高精度多普勒实时估计是水声通信系统的关键问题，使用双曲调频同步信号是一种解决方案。本文基于HFM信号的多普勒不变量和频谱特性的高精度、速度谱扫描方法

基于双HFM信号和速度谱扫描的多普勒估计

Doppler Estimation Based on Dual-HFM Signal and Speed Spectrum Scanning

Runyu Wei, Xiaochuan Ma, Shiduo Zhao, *Student Member, IEEE*, and Shefeng Yan, *Senior Member, IEEE*

***Abstract*—High-accuracy real-time Doppler estimation is one of the key problems in underwater acoustic communication systems. Using the dual-hyperbolic-frequency-modulation (dual-HFM) synchronous signal is an effective solution; however, the Doppler estimation accuracy is limited by the sampling frequency in the traditional methods. In this letter, we propose a high-accuracy speed spectrum scanning method based on the Doppler invariant and the frequency spectrum properties of the HFM signal. This signal processing system uses dual-HFM waveform as a synchronous signal, constructs the speed spectrum function at the receiver, and then obtains the Doppler estimate through one-dimensional scanning. This method breaks through the speed resolution limit induced by the sampling frequency in the traditional method and obtains a high-accuracy estimate. The influences of signal transmission and processing parameters on the Doppler estimation is analyzed, and the parameter selection criteria is presented to improve the reliability of the estimation. The results of both numerical simulation and underwater communication experiments prove the effectiveness of the proposed method.**

***Index Terms*—Doppler estimation, hyperbolic frequency modulation, underwater acoustic communication.**

I. Introduction

THE Doppler effect of underwater sound is much more severe than that of the radio for the propagation speed of sound waves is much slower than the speed of light. In areas such as underwater acoustic navigation, detection and confrontation, the Doppler estimation is an important part of the signal processor. In particular, in underwater acoustic communication and positioning systems, accurate real-time Doppler estimation is critical to the successful decoding of communication signals and the tracking of sound sources. Therefore, the issue of fast and high-accuracy Doppler estimation has received tremendous attention from researchers.

In underwater acoustic communication systems, Doppler estimation and compensation are required before demodulation [1]. The classical Doppler estimation method uses a set of correlators to calculate the correlation between different Doppler copies of the transmitted signal and the received signal, and the Doppler corresponding to the maximum correlation value is used as the estimate [1], [2]. While the resolution of this method increases as the number of correlators increases, the computational complexity increases significantly as well. Subsequently, researchers proposed a block Doppler estimation method [3]. In this scheme, two LFM signals are inserted before and after the data frame, and the two peaks outputted by the matched filters provide the estimate of the change in frame length, thereby obtaining the Doppler estimate. This method has been widely used and has been extended to variations such as the delayed cross-correlation method [4], [5]. However, this scheme loses real-time performance, and the estimation accuracy decreases significantly when the Doppler shift changes drastically during the processing period. The hyperbolic frequency modulation (HFM) signal is a Doppler-tolerant waveform that has been widely used by sonar systems [6]–[8]. In recent years, a Doppler estimation method based on two HFM signals with different frequency sweeping directions has gradually attracted attention [9]–[11]—this dual-HFM waveform is also called the Up-Mute-Down-HFM (UMD-HFM) signal [11]. While this method can realize fast real-time Doppler estimation, its performance is not robust in underwater acoustic channels. To fix this problem, a dual-HFM signal-based method using correlation peak matching (CPM) is proposed [12], which improves the robustness of traditional methods and has been experimentally verified. However, this method is designed based on time-domain correlators; thus, the Doppler resolution is limited by the sampling rate.

2)块多普勒估计方法，在数据帧之前和之后插入两个LFM信号，并且由匹配滤波器输出的两个峰值提供帧长度变化的估计，从而获得多普勒估计。缺点：不具有实时性

In view of the resolution limitation in the existing methods, a high-accuracy scheme for Doppler estimation based on the speed spectrum scanning is proposed in this letter. This method takes advantage of the Doppler invariance of the HFM signal and the frequency-domain properties of the differential HFM signal, allowing the radial speed estimate to be obtained through a one-dimensional search. Theoretical analysis shows that this method can achieve high-precision Doppler estimation under properly selected transmitting and processing parameters. Underwater communication experiments verify the effectiveness and the performance advantages of this method over the traditional dual-HFM signal-based methods.

The letter is organized as follows. Section II briefly introduces the theoretical basis of HFM signals. Section III derives and presents the proposed Doppler estimation method. Section IV shows the numerical simulation and underwater acoustic communication experiment results. Section V concludes with a brief summary.

HFM信号的性质

II. Properties of HFM Signal

The HFM signal waveform with start frequency f_l, end frequency f_h and pulse duration T is expressed as

$$s\left(f_l, f_h, T, t\right) = \mathrm{Rect}\left(\frac{t}{T}\right) \cdot \exp\left[-j2\pi \frac{f_0^2}{M} \ln\left(1 - \frac{M}{f_0}t\right)\right] \tag{1}$$

HFM信号波形：

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The authors are with the Key Laboratory of Information Technology for Autonomous Underwater Vehicles, the Institute of Acoustics, Chinese Academy of Sciences (IACAS), Beijing 100190, China, and also with the University of Chinese Academy of Sciences, Beijing 100864, China (e-mail: weirunyu@mail.ioa.ac.cn; maxc@mail.ioa.ac.cn; zhaoshiduo16@mails.ucas.edu.cn; sfyan@ieee.org).

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需要快速、高精度的多普勒估计的水声通信系统中，解调前需要多普勒估计和补偿。经典的多普勒估计方法是1)使用一组相关器计算发送信号和接收信号的不同多普勒副本间的相关性，并且对应于最大相关值的多普勒被用作估计值

where $j=\sqrt{-1}$. $f_0=\frac{2f_lf_h}{f_l+f_h}$ is the instantaneous frequency of the HFM signal at $t=0$, and $M=\frac{4f_lf_h(f_h-f_l)}{(f_l+f_h)^2\cdot T}$ is the frequency modulating factor. Under the premise that it will not cause confusion, f_l and f_h will be omitted, as they are always constant parameters in this letter. The instantaneous frequency of the HFM signal is

是一个双曲函数

HFM信号的瞬时频率：

$$f_t(T,t)=\frac{f_0}{1-\frac{M}{f_0}t}, \tag{2}$$

which is a hyperbolic function.

基于两个性质：HFM信号的多普勒不变性和差分HFM信号的谱特性

The Doppler estimation method proposed in this letter depends on two properties: the Doppler invariant property of the HFM signal and the spectral property of the differential HFM signal. The following is a brief introduction of these properties.

The HFM signal has similar properties to the LFM signal in narrow-band situation, but in wideband situation, the hyperbolic sweeping frequency makes the HFM signal "Doppler invariant" [13], [14]. When there is relative movement between the source and the receiver, the pulse width of the transmitted HFM signal is expanded, and the received waveform is

发送的HFM信号的脉冲宽度被扩展

$$s(kt)=\mathrm{Rect}\left(\frac{kt}{T}\right)\exp\left[-j2\pi\frac{f_0^2}{M}\ln\left(1-\frac{M}{f_0}\cdot kt\right)\right] \tag{3}$$

where $k=\frac{c}{c+v}$ is the scaling factor, v is the radial speed of the source away from the receiver, and c is the speed of sound. In active detection application scenarios, the scaling factor will be $k=\frac{c-v}{c+v}$. When $|v|/c$ is small, the difference between $\mathrm{Rect}(\frac{t}{T})$ and $\mathrm{Rect}(\frac{kt}{T})$ can be ignored, and

当|v|/c较小时，可以忽略Rect（t/T）和Rect（kt/T）之间的差异

$$s(kt)=s\left(t-\varepsilon(k)\right)\cdot\exp\left(j\vartheta(k)\right) \tag{4}$$

扩展信号几乎是原始HFM信号的时移。

is approximately satisfied on the definition domain, where $\varepsilon(k)=\frac{f_0}{M}(\frac{1}{k}-1)$ and $\vartheta(k)=-2\pi\frac{f_0^2}{M}\ln k$. Therefore, the expanded signal is almost a time-shift of the original HFM signal. After the expansion, the instantaneous frequency of the waveform is still a hyperbola with modulating factor M, despite the slight change in the sweeping frequency range. The difference between $\mathrm{Rect}(\frac{t}{T})$ and $\mathrm{Rect}(\frac{kt}{T})$ is influential only if the bandwidth is fairly small or if the radial speed is significantly large. An extended HFM matched filter was proposed to deal with this bias [15].

扩展后，波形的瞬时频率仍然是具有调制因子M的双曲线

尽管扫频范围略有变化。

The frequency spectrum of the HFM signal can only be accurately expressed by the incomplete gamma function [16]. However, the approximation within the frequency range (f_l,f_h) can be easily expressed. The use of (4) leads to an approximated spectrum within (f_l,f_h)

使用（4）可得到（fl，fh）内的近似频谱

$$S(T,f)=C(T)\cdot\frac{1}{f}\cdot\exp\left[j2\pi\frac{f_0}{M}\left(f_0\ln f-f+\varphi(T)\right)\right] \tag{5}$$

where $C(T)$ and $\varphi(T)$ are independent of f. For convenience, we will not expand these two factors. According to the Parseval's theorem, we have $\sqrt{\beta}C(T)=C(\beta T)$, where β is a positive real number. Making use of the derivative property of the Fourier transform, we obtain

利用傅里叶变换的导数性质，我们得到

$$-\frac{j}{2\pi\sqrt{\beta}}\exp\left(j\cdot\theta(T,\beta)\right)\cdot\left(C(T)\right)^{\beta-1}\cdot\frac{\mathrm{d}}{\mathrm{d}t}s(\beta T,t)=\mathcal{F}^{-1}\left[\left(f\cdot S(T,f)\right)^{\beta}\right] \tag{6}$$

where

$$\theta(T,\beta)=2\pi\frac{\beta f_0}{M}\left(\varphi(T)-\varphi(\beta T)\right) \tag{7}$$

is a factor independent of t. The differential HFM signal

差分HFM信号是：

$$\frac{\mathrm{d}}{\mathrm{d}t}s(T,t)=j2\pi f_t(T,t)\cdot s(T,t) \tag{8}$$

appearing on the left side of (6) is still a frequency modulation signal defined on $(-T/2,T/2)$, but its envelope $f_t(T,t)$ changes slowly (refer to (2)).

仍是定义在（-T/2，T/2）上的频调制信号，率但是包络缓慢变化（参考文献号

III. Doppler Estimation Based on Dual-HFM Signals

基于双HFM信号的多普勒估计

Let the transmit signal be the UMD-HFM signal defined in [11]

第一项是下扫HFM信号，第二项是上扫HFM信号

$$s_t(t)=s^{(\mathrm{d})}(f_h,f_l,T,t)+s\left(f_l,f_h,T,t-T-T_e\right) \tag{9}$$

as demonstrated in Fig. 1. The first term is a down-sweeping HFM signal and the second term is an up-sweeping HFM signal, and the whole signal is referred to as the "dual-HFM" signal in the following text. In this section, the superscript "(d)" represents the down-sweeping HFM signal, and the superscript "(u)" represents the up-sweeping HFM signal. Consider the case where the sound source is moving and the receiver is fixed. The received signal with Doppler effect can be expressed as

声源移动而接收器固定的情况下，具有多普勒效应的接收信号：

$$x(t)=A\cdot s_t\left(k\left(t-\tau\right)\right) \tag{10}$$

where A is the amplitude attenuation factor, $k=\frac{c}{c+v}$ is the waveform scaling factor, and τ is the propagation time (of the channel at $t=0$). From (4), the received signal can be expressed as the time-shifted form of the HFM source signal in equation (11) shown at the bottom of this page, where M is set as the positive (i.e. absolute) value. Let the frequency spectrum of the down-sweeping HFM signal be defined as

下扫HFM信号的频谱定义为：

$$S(f)=\mathcal{F}\left[s^{(\mathrm{d})}(T,t)\right] \tag{12}$$

The parameters of the transmit down-sweeping HFM signal are the default parameters when f_l, f_h and T are omitted in the followings. Since $\mathcal{F}[s^{(u)}(T,t)]=S^*(f)$, the absolute square spectrum of $x(t)$ can be written as equation (13) shown at the bottom of this page, where $\mathrm{Re}[\cdot]$ denotes the real part of the complex function, $\tau_1=-\varepsilon(k)$, and $\tau_2=\frac{1}{k}(T+T_e)+\varepsilon(k)$. To eliminate the influence of $S(f)$ and extract information about k, we define a statistic

为了消除S(f)的影响并提取k的信息，在(fl,fh)内定义一个统计量：

$$U(f)=f^4|X(f)|^2(S(f))^2 \tag{14}$$

HFM源信号的时移形式：

$$x(t)=A\cdot\left[s^{(\mathrm{d})}\left(T,t-(\tau-\varepsilon(k))\right)\cdot\exp\left(-j\vartheta(k)\right)+s^{(u)}\left(T,t-\left(\tau+\frac{1}{k}\left(T+T_e\right)+\varepsilon(k)\right)\right)\cdot\exp\left(j\vartheta(k)\right)\right] \tag{11}$$

（4），接收信号可以表示为式（11）的HFM信号的时移形式。

$$|X(f)|^2=2A^2\left\{|S(f)|^2+\mathrm{Re}\left[\left(S(f)\right)^2\cdot\exp\left(j2\pi f\left(\tau_2-\tau_1\right)\right)\cdot\exp\left(-j2\vartheta(k)\right)\right]\right\} \tag{13}$$

由于上扫HFM信号的傅里叶变换是下扫HFM傅里叶变换的复共轭，所以接收信号x(t)谱的模值的平方为式(13)

Δτ的估计可以从U（f）的傅里叶逆变换中获得

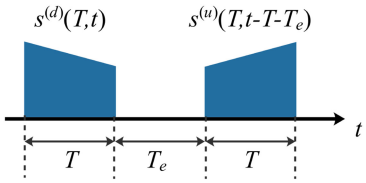


Fig. 1. Transmit signal structure.

式13、14、15包含周期为Δτ=τ2-τ1的复指数分量 发射信号的近似频谱

within the frequency range (f_l, f_h). From (5) we have $f^4 = C^4|S(f)|^{-4} = f^2C^2|S(f)|^{-2}$, where $C = C(T)$. Substituting it into (13) and (14) gives (15) shown at the bottom of this page, where, the last term includes the complex exponential component with period $\Delta\tau = \tau_2 - \tau_1$. Hence, the estimate of $\Delta\tau$ can be obtained from the inverse Fourier transform of $U(f)$. Making use of (6) we have (16) shown at the bottom of this page, where $\theta(2)$ and $\theta(4)$ are constants, and $\delta(t)$ is the impulse function. The first differential HFM signal is defined in $(-T, T)$, while the second one is defined in $(-2T - \Delta\tau, 2T - \Delta\tau)$. Let T_{seg} be the processing interval length when the time-domain signal is transformed into frequency domain. To ensure that neither the period $(-T, T)$ nor $(-2T - \Delta\tau, 2T - \Delta\tau)$ covers $t = \Delta\tau$, it should be satisfied that

为了让这俩都不覆盖t=Δτ，应满足：

$$T < \Delta\tau \text{ and } T_{seg} - 2T - \Delta\tau > \Delta\tau \tag{17}$$

Considering that $\Delta\tau \approx T + T_e$ when $|v| \ll c$, then (17) reduces to

满足这两个条件时：(16前两项对Δτ估计的影响将基本消除。

$$T_e > 0 \tag{18}$$

$$T_{seg} > 4T + 2T_e = 2(2T + T_e) \tag{19}$$

and the two inequalities should keep a certain margin. The inequality (18) suggests that there should be a gap between the down-sweeping and the up-sweeping HFM signals in the transmit waveform. The inequality (19) suggests that the signal should be extended to at least twice as long as the transmit waveform by padding zero before being transformed into the frequency domain. When these two inequalities are both satisfied, the impact of the first two terms in (16) in regards to the estimation of $\Delta\tau$ will be mostly eliminated.

However, because the time resolution of the IFFT output cannot be higher than the sampling interval, the accuracy of the estimated value of $\Delta\tau$ may not be ideal. Since the speed is $v = \frac{c\Delta\tau}{T+T_e+2f_0/M}$, the estimation error of the speed is

由于IFFT输出的时间分辨率不能高于采样间隔，Δτ估计值的精度可能不理想，速度表达式各异，速度的估计误差是：

$$e(v) = \frac{c}{T + T_e + 2f_0/M} \cdot e(\Delta\tau) \tag{20}$$

Thus, the resolution unit of the speed estimate derived from the IFFT method is $\epsilon_v = \frac{c}{T+T_e+2f_0/M} \cdot \frac{1}{f_s}$, where f_s is the sampling frequency. Therefore, the resolution of the speed estimate is limited by the sampling frequency. 速度估计的分辨率受到采样频率的限制

Using high-resolution line spectral estimation methods can obtain speed estimations with resolution higher than ϵ_v. Since there is only one periodic component in (15), the best estimate

使用高分辨率线谱估计方法可以获得分辨率高于上面这个方法的速度估计值

因此，IFFT方法导出的速度估计的分辨率单位是

$$U(f) = A^2\left\{2C^2(f\cdot S(f))^2 + (f\cdot S(f))^4\cdot\exp\left(j2\pi f\left(\tau_2-\tau_1\right)\right)\cdot\exp\left(-j2\vartheta(k)\right)\right\} + C^4\exp\left(-j2\pi f\left(\tau_2-\tau_1\right)\right)\cdot\exp\left(j2\vartheta(k)\right) \tag{15}$$

这是那仅有的一个周期分量？

$$\mathcal{F}^{-1}\left[U(f)\right] = A^2C^3\left\{-\frac{j}{4\pi}\left[\begin{array}{l}2\sqrt{2}\exp\left(j\cdot\theta(2)\right)\cdot\frac{\mathrm{d}}{\mathrm{d}t}s^{(d)}\left(2T,t\right)\\+\exp\left(j\cdot\theta(4)\right)\cdot\frac{\mathrm{d}}{\mathrm{d}t}s^{(d)}\left(4T,t+\Delta\tau\right)\end{array}\right] + C\delta\left(t-\Delta\tau\right)\cdot\exp\left(j2\vartheta(k)\right)\right\} \tag{16}$$

满足这两个条件时，前面这两项对于Δτ估计基本没影响了

由于(fl,fh)外主要是噪声，15最后一项很难是的正弦函数

速度谱扫描是小范围内（14）的IDFT，这打破了IFFT对（14）分辨率的限制。一个可行的方法是首先使用IFFT进行粗略搜索，然后使用频谱扫描进行高精度搜索。

通过扫描以径向速度为自变量的“速度谱”，可以简单地获得周期信息。

of periodic information can be simply obtained by scanning the "speed spectrum" with radial speed as the independent variable. In other words, assume that the possible range of the speed is (v_1, v_2), and then scan the spectrum with all the possible speeds within the range. Define the speed spectrum function as

假设速度的可能范围是（v1，v2），然后用该范围内的所有可能速度扫描频谱。将速度谱函数定义为

$$Y(v) = \int_f U(f)\exp\left(j2\pi f\left(c_1v + c_2\right)\right)\mathrm{d}f \tag{21}$$

where $c_1 = \frac{(T+T_e)+2f_0/M}{c}$ and $c_2 = T + T_e$ are both constants. The estimate of the radial speed is

估计的径向速度：$\hat{v} = \arg\max_{v\in(v_1,v_2)}|Y(v)|$ (22)

In fact, the speed spectrum scanning is the IDFT of (14) within a small range, which breaks the resolution limitation of IFFT on (14). A practicable procedure is to use IFFT for a rough search first, and then use spectrum scanning for high-precision search. It should be noted that the frequency-domain processing above is calculated within the frequency range (f_l, f_h) (or a little bit expanded according to [15]), and the components outside the range should set zero. This is because the frequency spectrum expression of the HFM signal given in Section II is only appropriate within the range (f_l, f_h). Moreover, since the received signal out of this range is mostly noise, the last term of (15) can hardly be a sinusoidal function outside the frequency range.

The steps in the proposed speed spectrum scanning algorithm can be summarized as follows: 所提出的速度扫描谱的扫描算法总结如下：

1) Find the approximate location of the dual-HFM waveform in the received signal using matched filtering, and intercept a segment of signal containing the dual-HFM signal. Extend the intercepted signal segment to length T_{seg} by padding zero where $T_{seg} > 2(2T + T_e)$, and reserve a certain margin.
2) Calculate the frequency spectrum $X(f)$ of the zero-padded signal, and calculate the statistic $U(f)$ given by expression (14), where $X(f)$ is determined by (12). Note that the down-sweeping HFM signal should be extended to the same length as $X(f)$ by padding zero. If the bandwidth is not large enough or the Doppler shift is significant, the bandwidth can be appropriately increased [15] when calculating (12).
3) Scan the radial speed within the possible range of speed and calculate the speed spectrum $Y(v)$ defined by (21). The radial speed estimate $\hat{v}$ is given by (22).

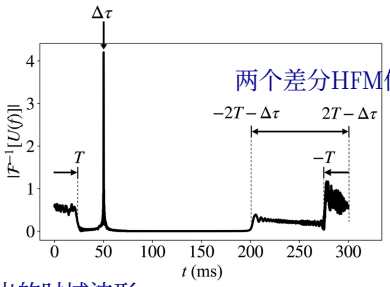
仿真和实验结果

IV. Simulation and Experimental Results

In this section, we present numerical simulation and underwater experimental results of the proposed Doppler estimation method. The underwater experiment is designed to test the reliability of the underwater communication system and the positioning performance of the multi-buoy network for underwater moving sources. The methods to be compared are matched-filter-based traditional method and CPM method, and [9], [12] provide a detailed introduction about them.

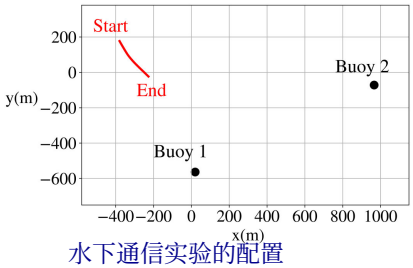
要比较的方法是基于匹配滤波的传统方法和CPM方法

峰值



输出的时域波形

Fig. 2. IFFT result of $U(f)$ (without noise).

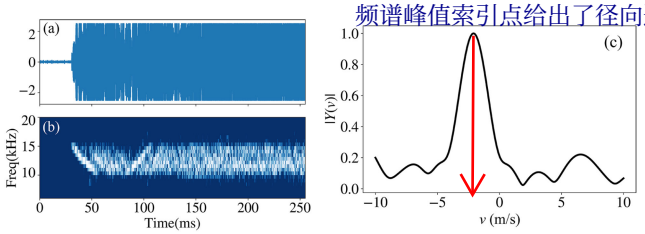


水下通信实验的配置

Fig. 3. Underwater communication experiment configuration.

通滤波后

时频图



频谱峰值索引点给出了径向速度估计值

Fig. 4. (a, b) Received waveform and spectrogram; (c) The speed spectrum $|Y(v)|$ of underwater moving source (actual speed: $v_{real} = -2.13$ m/s).

首先，通过数值模拟证明了无噪声的F-－1[U（F）
质，计算机模拟中的参数设置如下：产

Firstly, the properties of $\mathcal{F}^{-1}[U(f)]$ without noise are demonstrated by numerical simulation. The parameters used in the computer simulation are as follows: dual-HFM signal parameters $f_l = 4$ kHz, $f_h = 8$ kHz, $T = T_e = 25$ ms, $f_s = 50$ kHz; speed parameters $v = 2$ m/s, $c = 1500$ m/s; signal processing parameter $T_{seg} = 300$ ms. After calculating $U(f)$ with (14) and performing IFFT, the output time-domain signal is shown in Fig. 2. It can be seen that the peak of $|\mathcal{F}^{-1}[U(f)]|$ is approximately at $\Delta\tau \approx T + T_e$, and two differential HFM signals are located at $(-T, T)$ and $(-2T - \Delta\tau, 2T - \Delta\tau)$, respectively. The numerical simulation result under ideal noiseless conditions verifies the deduction in (16). Therefore, appropriate selection of signal transmission and processing parameters can effectively avoid the influence of the two differential HFM signals on the detection of the periodic component in $U(f)$.

Next, a set of experimental sonar data is used to test the proposed Doppler estimation method. The field trial data was collected in Thousand Island Lake, China, in March 2018. As shown in Fig. 3, the transducer mounted 3 m-deep moved along the trajectory at an average speed 2.15 m/s, and two hydrophones (approximately 1.5 m deep) were attached to buoys. The actual position of the transducer and the buoys are provided by GPS. The source transmitted communication data frames every 2 seconds with dual-HFM signal as the preamble. The transmission parameters are: $f_l = 10$ kHz, $f_h = 15$ kHz, $T = T_e = 25.6$ ms, and $f_s = 80$ kHz.

千岛湖实验数据；信号源以双HFM信号作为前导
码

适当选择信号传输和处理参数可以有效避免两个差
分HFM信号对U（f）中周期分量检测的影响。

我们处理了来自两个浮标的连续60帧数据。径向速
度估计结果如图5所示

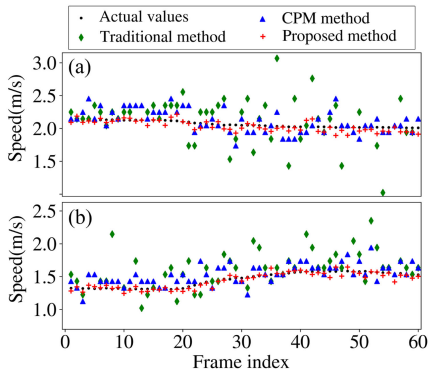


Fig. 5. Estimation results of target radial speed (60 frames).

TABLE I
RMSE OF THE RADIAL SPEED ESTIMATES (M/S)

	Buoy 1	Buoy 2
Traditional method	1.394	1.417
CPM method	0.159	0.147
Proposed method	0.060	0.046

以浮标1的接收帧为例

Taking a received frame of buoy 1 as an example, Fig. 4(a) shows the waveform after bandpass filtering, and Fig. 4(b) shows the time-frequency spectrogram. The dual-HFM signal can be observed in the spectrogram. We process the intercepted signal using the proposed method, where $T_{seg} = 300$ ms and the speed scanning range is $(-10$ m/s, 10 m/s$)$. The result of $|Y(v)|$ is given in Fig. 4(c). The spectrum peak gives the radial speed estimate $\hat{v} = -2.092$ m/s, while the actual value from GPS data is $v_{real} = -2.13$ m/s.

Using the method proposed above, we process the continuous 60 frames of data from the two buoys. The radial speed estimation results are plotted in Fig. 5, where the speed of the source moving closer to the receiver is defined as positive. The traditional method and the CPM method are employed for comparison. The root mean square error (RMSE) of the estimates are given in Table I, and Fig. 5 and Table I show that the proposed method shows a further improvement in estimation performance than the methods introduced in [12]. The performance improvement comes from two aspects: on the one hand, the appropriate transmission and processing parameters reduce the interference in the peak detection; on the other hand, the speed spectrum scanning breaks through the resolution limit ϵ_v, and achieves the continuous estimation of the target speed.

性能的提高来自两个方面：一方面，适当的传输和
处理参数减少了峰值检测中的干扰；另一方面，频
谱(速度谱)扫描速度突破了分辨率极限 并且实现目
标速度的连续估计。

V. CONCLUSION

In this letter, we introduce a novel Doppler estimation method based on the dual-HFM signal and speed spectrum scanning. Through theoretical analysis, appropriate transmission and processing parameters are selected, reducing the interference in speed spectrum peak detection and thereby increasing the accuracy of the estimation. In addition, the speed spectrum scanning breaks through the speed resolution limit by the sampling frequency and realizes the continuous estimation. The numerical simulation and the underwater communication experiment verify the effectiveness of the method, as well as the application prospect of the dual-HFM signal in the field of underwater communication synchronization and underwater target detection and tracking.

介绍了一种基于双HFM信号和速度谱扫描的多普勒估计
方法。
通过理论分析，选择了合适的传输和处理参数，减少了
速度谱峰值检测中的干扰，从而提高了估计的准确性。
此外，速度谱扫描突破了采样频率对速度分辨率的限制
实现了连续估计。

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