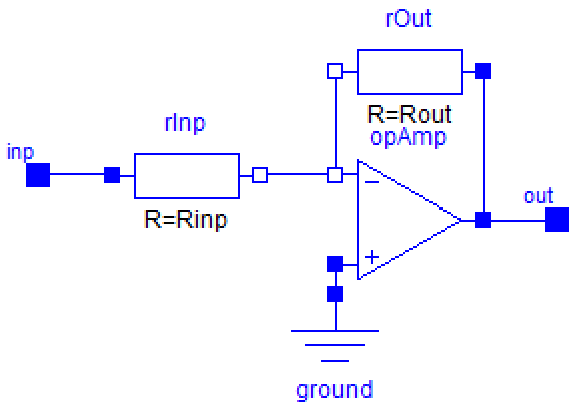
OpAmp-Circuits

Amplifier/Adder



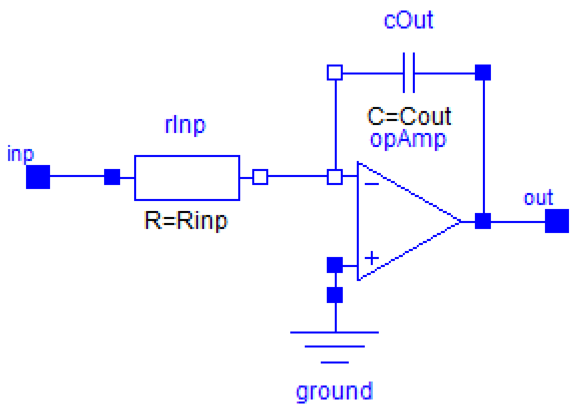
$$\frac{inp.v}{R_{inp}} + \frac{out.v}{R_{out}} = 0$$

$$-out.v = k \cdot inp.v$$

$$k = \frac{R_{out}}{R_{inp}}$$

It is possible to add several inputs.

Integrator



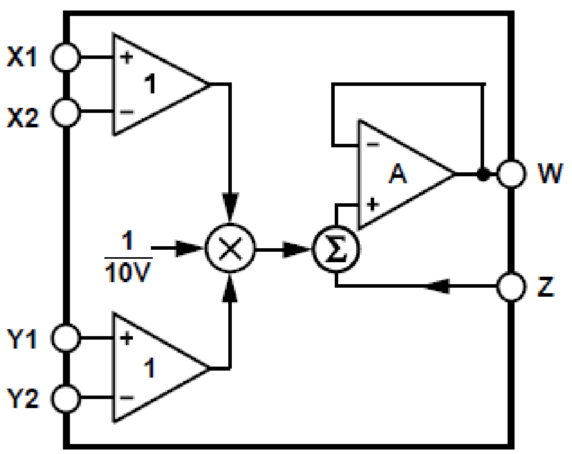
$$\frac{inp.v}{R_{inp}} + C_{out} \cdot \frac{d\ out.v}{dt} = 0$$

$$-out.v = v_0 + \frac{1}{\tau} \cdot \int_0^t inp.v \cdot dt$$

$$\tau = R_{inp} \cdot C_{out}$$

It is possible to integrate the sum of several inputs.

Analog Multiplier



Functional Block Diagram of AD633
Division by $10\ V$ (scaling) inhibits overflow.
Additional summing input Z is omitted.
Negative inputs of X- and Y-amplifiers are connected to ground.

Possible implementations:

- Gilbert cell
- $y = e^{ln(x_1)+ln(x_2)}$
- $y = \frac{(x_1+x_2)^2-(x_1-x_2)^2}{4}$

1_Lotka-Volterra

https://en.wikipedia.org/wiki/Lotka%E2%80%93Volterra_equations

https://en.wikipedia.org/wiki/Competitive_Lotka%E2%80%93Volterra_equations

https://sprott.physics.wisc.edu/pubs/paper288.pdf

As a 2-dimensional predator-prey-model no chaos is reported:

$$\frac{dx}{dt} = r_x \cdot x - d_x \cdot x \cdot y$$
$$\frac{dy}{dt} = r_x \cdot x \cdot e_y \cdot y - d_y \cdot y$$

We might interpret x as number of hares (prey) and y as foxed (predator).
r_x is the reproduction rate of hares, d_x the deathrate of hares due to foxes.

e_y is the efficiency in growing foxes from hares, d_y the (natural) deathrate of foxes.

A n-dimensional Lotka-Volterra model is defined for $1 \leq i \leq n$ (n designates the number of species):

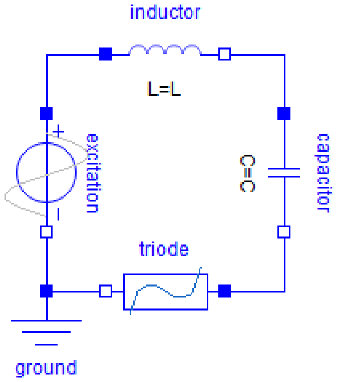
$$\frac{dx_i}{dt} = r_i \cdot x_i \cdot \left(1 - \sum_{j=1}^{n} a_{ij} \cdot x_j\right)$$

The vector $[r]$ describes the reproduction rates of the species whereas the quadratic matrix $[a]$ describes the competition between species.

2 van der Pol Circuit

https://en.wikipedia.org/wiki/Van_der_Pol_oscillator
B. van der Pol and J. van der Mark, „Frequency Demultiplication”, Nature 120 (1927), p. 363-364, ISSN 0028-0836, DOI https://doi.org/10.1038/120363a0

Balthasar van der Pol reported 1927 strange phenomena about oscillations in a series resonance circuit containing a vacuum electron triode. Due to the nonlinear characteristic of the triode the autonomous circuit is able to maintain periodic oscillations, and with harmonic excitation it is able to produce chaos.



$$i = C \cdot \frac{dv_C}{dt} \rightarrow v_C = v_{C0} + \frac{1}{C} \cdot \int_{t_0}^{t} t \cdot dt'$$

$$L \cdot \frac{di}{dt} + \tilde{R}(i) \cdot i + v_C = \begin{cases} 0 \\ \hat{V} \cdot cos(\omega \cdot t - \pi) \end{cases}$$

$$\tilde{R}(i) = -R_0 \cdot \left[1 - \frac{1}{3} \cdot \left(\frac{i}{I_0}\right)^2\right]$$

$$L \cdot \frac{d^2 i}{dt^2} - R_0 \cdot \left[1 - \left(\frac{i}{I_0}\right)^2\right] \cdot \frac{di}{dt} + \frac{1}{C} \cdot i = \begin{cases} 0 \\ \hat{V} \cdot \omega \cdot sin(\omega \cdot t) \end{cases}$$

$$\omega_0 = \frac{1}{\sqrt{L \cdot C}}$$

$$\mu = R_0 \cdot \sqrt{\frac{C}{L}}$$

$$A = \frac{\omega \cdot C \cdot \hat{V}}{I_0}$$

$$w = \frac{\omega}{\omega_0}$$

$$\tau = \omega_0 \cdot t$$

$$x = \frac{i}{I_0}$$

$$y = \frac{dx}{d\tau} = \frac{1}{\omega_0 \cdot I_0} \cdot \frac{di}{dt}$$

$$\frac{I_0}{\omega_0 \cdot C} \cdot z = v_C = v_{C0} + \frac{1}{C} \cdot \int_{t_0}^{t} i \cdot dt'$$

$$z = z_0 + \int_{\tau_0}^{\tau} x \cdot d\tau'$$

$$\frac{d^2 x}{d\tau^2} - \mu \cdot [1 - x^2] \cdot \frac{dx}{d\tau} + x = \begin{cases} 0 \\ A \cdot sin(w \cdot \tau) \end{cases}$$

$$\frac{dx}{d\tau} = y$$

$$\frac{dy}{d\tau} = \mu \cdot [1 - x^2] \cdot y - x + \begin{cases} 0 \\ A \cdot sin(w \cdot \tau) \end{cases}$$

$$\frac{dz}{d\tau} = x$$

Initialization:
The physical model has 2 states: i and v_C. Current i acts as an initial value for the nonlinear resistor.
The analytic equations have 3 states: x, y and z.
The third state has been introduced artificially by first differentiating the voltage equation, generating an equation with second derivative of i. Splitting this equation into two first order differential equations, we generate i and $\frac{di}{dt}$ as states. Calculating capacitor voltage v, we get the third state.
To compare the results of the physical model and the analytic equations, the initial conditions would have to be equivalent. This makes comparability difficult.

For an implementation as an electronic circuit, the equations have to be scaled to keep the variables within the desired range.

$$x' = \frac{x}{k_x}$$
$$y' = \frac{y}{k_y}$$
$$z' = \frac{z}{k_z}$$
$$t' = \frac{\tau}{\omega_0}$$

We also have to take into account that the analog multiplier divides by V_S to avoid overflow of the output. After that, none of the computing block should encounter an overflow.
This leads to the following set of equations:

$$\frac{1}{\omega_0} \cdot \frac{dx'}{dt'} = \frac{k_y}{k_x} \cdot y$$
$$\frac{1}{\omega_0} \cdot \frac{dy'}{dt'} = \mu \cdot \left[\frac{1}{{k_x}^2 \cdot V_S} - \frac{{x'}^2}{V_S}\right] {k_x}^2 \cdot {V_S}^2 \cdot \frac{y'}{V_S} - \frac{k_x}{k_y} \cdot x' + \frac{1}{k_y} \cdot A \cdot sin(w \cdot \omega_0 \cdot t')$$

The implementation of the differential equation of the capacitor's voltage could be omitted:

$$\frac{1}{\omega_0} \cdot \frac{dz'}{dt'} = \frac{k_x}{k_y} \cdot x'$$

These equations can easily get implemented as blocks or as an electronic circuit.

Calculating back from per-unit-parameters:

$$\mu = 0.2, w = 1.15, A = [0..1]$$

and some assumptions:

$$C = \frac{100}{2\pi}\ \mu F, \omega_0 = 2\pi \cdot 1000\ \frac{rad}{s}, I_0 = 0.5\ A$$

we obtain physical parameters:

$$L = \frac{1}{{\omega_0}^2 \cdot C} = \frac{10}{2\pi}\ mH$$
$$R_0 = \mu \cdot \sqrt{\frac{L}{C}} = \frac{\mu}{\omega_0 \cdot C} = 2\ \Omega$$
$$\hat{V} = A \cdot \frac{I_0}{w \cdot \omega_0 \cdot C} = \left[0 \cdots \frac{25}{6}\right]\ V$$

Investigating the nonlinear resistance of the triode:

$$v_R = -R_0 \cdot I_0 \cdot \left[\left(\frac{i}{I_0}\right) - \frac{1}{3} \cdot \left(\frac{i}{I_0}\right)^3\right] = -R_0 \cdot i \cdot \left[1 - \frac{1}{3} \cdot \left(\frac{i}{I_0}\right)^2\right]$$

$$\frac{v_R}{i} = -R_0 \cdot \left[1 - \frac{1}{3} \cdot \left(\frac{i}{I_0}\right)^2\right]$$

$$\frac{dv_R}{di} = -R_0 \cdot \left[1 - \left(\frac{i}{I_0}\right)^2\right]$$

$$x = \frac{i}{I_0}$$

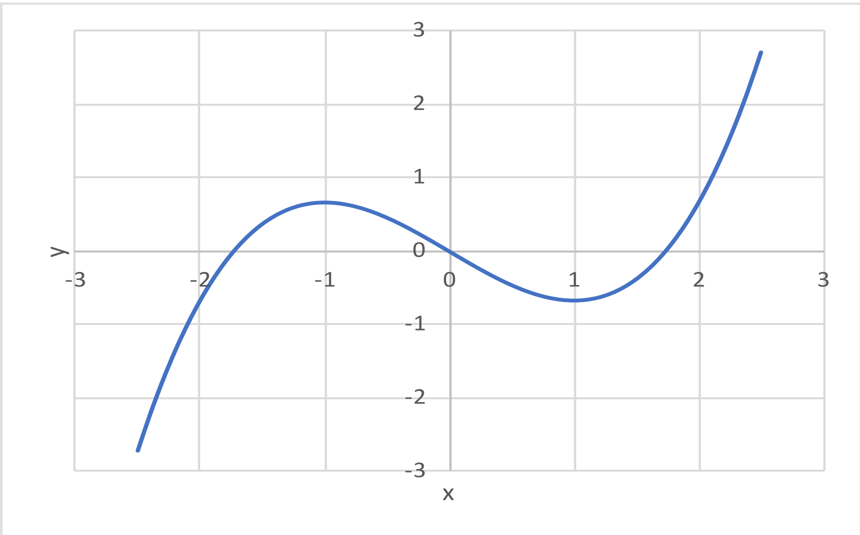
$$y = \frac{v_R}{R_0 \cdot I_0}$$

$$y = -\left(x - \frac{x^3}{3}\right) = -x \cdot \left(1 - \frac{x^2}{3}\right)$$

$$\frac{y}{x} = -\left(1 - \frac{x^2}{3}\right)$$

$$\frac{dy}{dx} = -(1 - x^2)$$

Characteristic of the triode $y(x)$:



Zero crossings $y = 0$: $x = \{-\sqrt{3}, 0, +\sqrt{3}\}$ with slopes $\frac{dy}{dx} = \{+2, -1, +2\}$

Extrema: $x = \{-1, +1\}$ with $x = \left\{+\frac{2}{3}, -\frac{2}{3}\right\}$

Inflection point: $[x, y] = [0, 0]$

If current x is prescribed, voltage y can be unambiguously determined.

If y is prescribed, in the range $-2 \leq x \leq +2$ i.e. $-\frac{2}{3} \leq y \leq +\frac{2}{3}$ x has 2 or 3 possible solutions.

For this application, this restriction has no influence.

Shifting the characteristic up and to the right, it looks like the $i(v)$ characteristic of a tunnel (Esaki) diode.

Note:

Instead of using a series resonance circuit and deriving a scaled differential equation for the current, we could use an equivalent parallel resonance circuit and derive a scaled differential equation for the voltage.

3_Lorenz System

http://en.wikipedia.org/wiki/Lorenz_attractor
Developed 1963 by Edward Lorenz to model atmospheric convection.
x is proportional to the rate of convection, y to the horizontal temperature variation and z to the vertical temperature variation. σ depicts the Prandtl number, ρ the Rayleigh number and β the physical dimensions.
The original parameters were: $\sigma = 10, \rho = 28, \beta = \frac{8}{3}$

$$\frac{dx}{dt} = \sigma \cdot (y - x)$$
$$\frac{dy}{dt} = x \cdot (\rho - z) - y$$
$$\frac{dz}{dt} = x \cdot y - \beta \cdot z$$

$\beta = \frac{1}{3}$ leads to a periodic solution.

For an implementation as an electronic circuit, the equations have to be scaled to keep the variables within the desired range. This can be compared with calculating per-unit values by dividing by reference values:

$$x' = \frac{x}{k_x}$$
$$y' = \frac{y}{k_y}$$
$$z' = \frac{z}{k_z}$$
$$t' = \frac{t}{\tau}$$

We also have to take into account that the analog multiplier divides by V_S to avoid overflow of the output. After that, none of the computing block should encounter an overflow.
This leads to the following set of equations:

$$\frac{1}{\tau} \cdot \frac{dx'}{dt'} = -\sigma \cdot x' + \sigma \cdot \frac{k_y}{k_x} \cdot y'$$
$$\frac{1}{\tau} \cdot \frac{dy'}{dt'} = \rho \cdot \frac{k_x}{k_y} \cdot x' - y' - \frac{k_x \cdot k_z \cdot V_S}{k_y} \cdot \frac{x' \cdot z'}{V_S}$$
$$\frac{1}{\tau} \cdot \frac{dz'}{dt'} = \frac{k_x \cdot k_y \cdot V_S}{k_z} \cdot \frac{x' \cdot y'}{V_S} - \beta \cdot z'$$

These equations can easily get implemented as blocks or as an electronic circuit.

4_Roessler System

https://en.wikipedia.org/wiki/R%C3%B6ssler_attractor

A simple system of 3 ordinary nonlinear differential equations to study chaos without physical background.

$$\frac{dx}{dt} = -y - z$$
$$\frac{dy}{dt} = x + a \cdot y$$
$$\frac{dz}{dt} = b + (x - c) \cdot z$$

$a = 0.2$, $b = 0.2$ and $c = 1$ give periodic results. Changing $c = 5.7$ reveals chaotic results.

For an implementation as an electronic circuit, the equations have to be scaled to keep the variables within the desired range. This can be compared with calculating per-unit values by dividing by reference values:

$$x' = \frac{x}{k_x}$$
$$y' = \frac{y}{k_y}$$
$$z' = \frac{z}{k_z}$$
$$t' = \frac{t}{\tau}$$

We also have to take into account that the analog multiplier divides by V_S to avoid overflow of the output. After that, none of the computing block should encounter an overflow.

This leads to the following set of equations:

$$\frac{1}{\tau} \cdot \frac{dx'}{dt} = -\frac{k_y}{k_x} \cdot y' - \frac{k_z}{k_x} \cdot z'$$
$$\frac{1}{\tau} \cdot \frac{dy'}{dt} = \frac{k_x}{k_y} \cdot x' + a \cdot y'$$
$$\frac{1}{\tau} \cdot \frac{dz'}{dt} = \frac{b}{k_z} + k_x \cdot V_S \cdot \frac{x' \cdot z'}{V_S} - c \cdot z'$$

These equations can easily get implemented as blocks or as an electronic circuit.

5_Chua's Circuit

https://link.springer.com/book/10.1007/978-3-319-05900-6 (1.1)

https://nonlinear.eecs.berkeley.edu/chaos/chaos.html#_Working_With_Chaos_Simulation

$$L \cdot \frac{di_L}{dt} = v_2 - R_L \cdot i_L$$

$$C_2 \cdot \frac{dv_2}{dt} = -i_L - \frac{v_2 - v_1}{R}$$

$$C_1 \cdot \frac{dv_1}{dt} = -i_{NL} + \frac{v_2 - v_1}{R}$$

$$-i_{NL}(v_1) = \begin{cases} -\infty < v_1 < -V_e \to G_b \cdot (v_1 + V_e) - G_a \cdot V_e \\ -V_e < v_1 < +V_e \to G_a \cdot v_1 \\ +V_e < v_1 < +\infty \to G_b \cdot (v_1 - V_e) + G_a \cdot V_e \end{cases}$$

$$-\frac{i_{NL}}{v_1} = \begin{cases} -\infty < v_1 < -V_e \to G_b - (G_a - G_b) \cdot \dfrac{V_e}{v_1} \\ -V_e < v_1 < +V_e \to G_a \\ +V_e < v_1 < +\infty \to G_b + (G_a - G_b) \cdot \dfrac{V_e}{v_1} \end{cases}$$

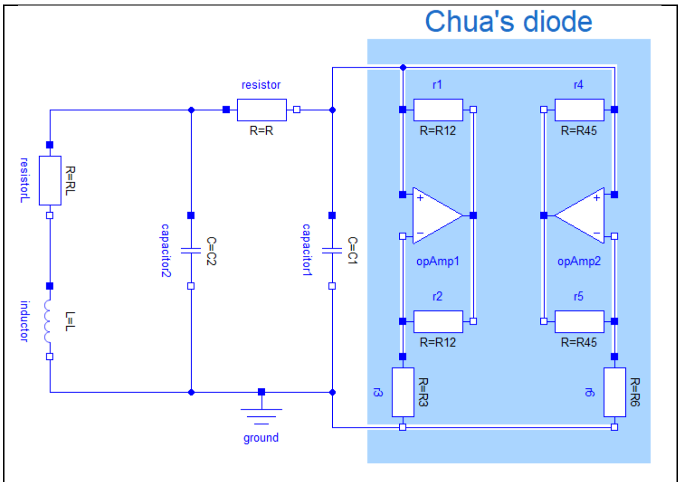
$$-\frac{di_{NL}}{dv_1} = \begin{cases} -\infty < v_1 < -V_e \to G_b \\ -V_e < v_1 < +V_e \to G_a \\ +V_e < v_1 < +\infty \to G_b \end{cases}$$

$$\tau_L \cdot \dot{v}_{RL} = v_2 - v_{RL}$$

$$\tau_2 \cdot \dot{v}_2 = +v_1 - v_2 - \frac{R}{R_L} \cdot v_{RL}$$

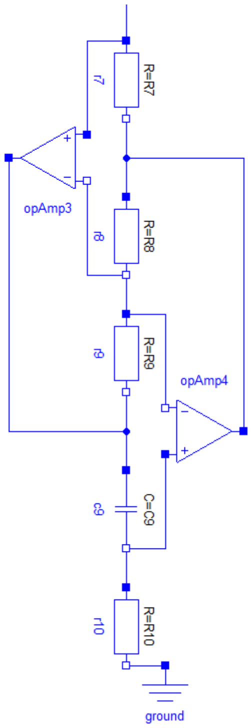
$$\tau_1 \cdot \dot{v}_1 = -v_1 + v_2 + R \cdot g \cdot v_1$$

$$g(v_1) = \begin{cases} |v_1| > V_e \to G_b + (G_a - G_b) \cdot \dfrac{V_e}{|v_1|} \\ |v_1| < V_e \to G_a \end{cases}$$




```
parameter SI.Resistance R=1.9e3 "Resistor";
parameter SI.Inductance L=18e-3 "Inductor";
parameter SI.Resistance RL=14 "Resistance of Inductor";
parameter SI.Capacitance C1=10.e-9 "Capacitor 1";
parameter SI.Capacitance C2=100e-9 "Capacitor 2";
//parameter of Chua's diode
parameter Real k0=15000.0 "No-load amplification ";
parameter SI.Voltage Vs=9 "Supply voltage of opAmps";
parameter SI.Resistance R12=220 "R1 and R2";
parameter SI.Resistance R3=2200 "R3";
parameter SI.Resistance R45=22e3 "R4 and R5";
parameter SI.Resistance R6=3300 "R6";
```

Chua's Circuit: Inductor Replacement



$$R_7 = 100\ \Omega$$
$$R_8 = 1\ k\Omega$$
$$R_9 = 1\ k\Omega$$
$$R_{10} = 1{,}8\ k\Omega$$
$$C_9 = 100\ nF$$

$$R_7 \cdot i + R_8 \cdot (i + i_{OA4}) = 0$$
$$R_9 \cdot (i + i_{OA4}) + v_{c9} = 0$$
$$i + i_{OA4} + i_{OA3} = i_{C9}$$
$$i_{C9} = C_9 \cdot \frac{dv_{C9}}{dt}$$
$$v = R_{10} \cdot i_{C9}$$

$$(i + i_{OA4}) = -\frac{R_7}{R_8} \cdot i$$
$$v_{c9} = \frac{R_7 \cdot R_9}{R_8} \cdot i$$
$$i_{C9} = C_9 \cdot \frac{R_7 \cdot R_9}{R_8} \cdot \frac{di}{dt}$$
$$v = C_9 \cdot \frac{R_7 \cdot R_9 \cdot R_{10}}{R_8} \cdot \frac{di}{dt}$$

$$\boxed{L = C_9 \cdot \frac{R_7 \cdot R_9 \cdot R_{10}}{R_8} = 18\ mH}$$

6_Chaotic Diode Circuit

https://www.researchgate.net/publication/309351711_A_simple_chaotic_circuit_with_a_light-emitting_diode

$$C \cdot \frac{dv_1}{dt} = -\frac{v_2}{R}$$

$$C \cdot \frac{dv_2}{dt} = -\frac{v_3}{R}$$

$$C \cdot \frac{dv_3}{dt} = -\frac{v_1}{R} - \frac{v_3}{R_b} - \frac{v_4}{R}$$

$$\frac{v_4}{R_a} = -I_{ds} \cdot \left(e^{\frac{v_2}{nV_t}} - 1\right)$$

$$\tau = R \cdot C$$

$$\tau \cdot \frac{dv_1}{dt} = -v_2$$

$$\tau \cdot \frac{dv_2}{dt} = -v_3$$

$$\tau \cdot \frac{dv_3}{dt} = -v_1 - \frac{R}{R_b} \cdot v_3 + R_a \cdot I_{ds} \cdot \left(e^{\frac{v_2}{nV_t}} - 1\right)$$

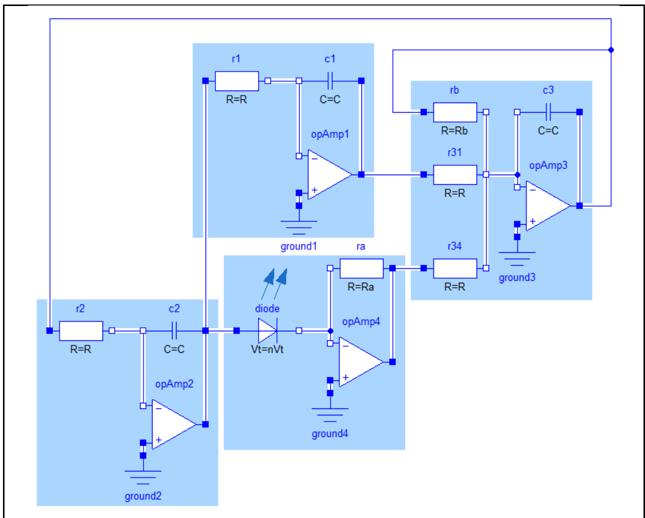
$$a = \frac{R_a \cdot I_{ds}}{nV_t}$$

$$b = \frac{R}{R_b}$$

$$\tau \cdot \dot{x}_1 = -x_2$$

$$\tau \cdot \dot{x}_2 = -x_3$$

$$\tau \cdot \dot{x}_3 = -x_1 + a \cdot (e^{x_2} - 1) - b \cdot x_3$$




```
parameter SI.Current Ids=1e-9 "Diode: saturation current";
parameter SI.Voltage nVt=2*26e-3
" n*voltage equ. of temperature";
//time constant and dimensionless parameters
parameter SI.Time Tau=0.1e-3 "Time constant";
parameter Real a=1/5200 "Parameter a = Ra*Ids/nVt";
parameter Real b=1.5 "Parameter b = R/Rb";
//configuration of the opAmps
parameter SI.Capacitance C=10e-9
"Capacitance of {c1, c2, c3}";
parameter SI.Resistance R=Tau/C "Resistance of {r1,r2,r3,r4}";
parameter SI.Resistance Ra=a*nVt/Ids "Resistance of ra";
parameter SI.Resistance Rb=R/b "Resistance of rb";
```

7_Chaotic Oscillator

https://www.researchgate.net/publication/230925506_A_simple_chaotic_oscillator_for_educational_purposes

https://www.researchgate.net/publication/259216097_NUMERICAL_TREATMENT_OF_EDUCATIONAL_CHAOS_OSCILLATOR

$$i_L = C \cdot \frac{dv_C}{dt}$$

$$L \cdot \frac{di_L}{dt} = \left(k - 1 - \frac{R_L}{R}\right) \cdot R \cdot i_L - v_C - v_{C^*}$$

$$k = 1 + \frac{R_2}{R_1}$$

$$C^* \cdot \frac{dv_{C^*}}{dt} = I_0 + i_L - I_{DS} \cdot \left(e^{\frac{v_{C^*}}{nV_t}} - 1\right)$$

$$I_0 \approx \frac{V_b}{R_0}$$

$$\tau = \sqrt{L \cdot C}$$

$$Z = \sqrt{\frac{L}{C}}$$

$$a = \left(k - 1 - \frac{R_L}{R}\right) \cdot \frac{R}{Z}$$

$$b = \frac{Z \cdot I_0}{nV_t}$$

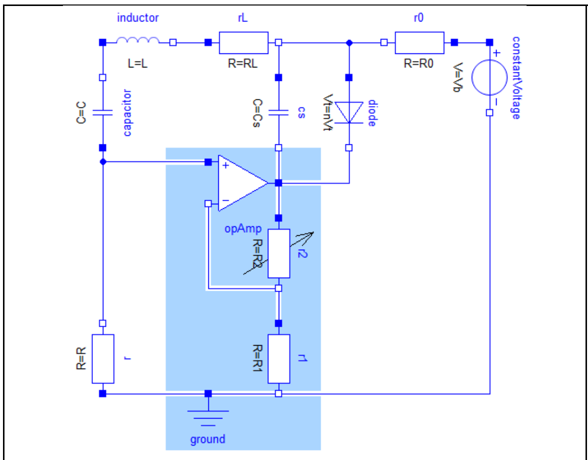
$$c = \frac{Z \cdot I_{DS}}{nV_t}$$

$$e = \frac{C^*}{C}$$

$$\tau \cdot \frac{\dot{v}_C}{nV_t} = \frac{Z \cdot i_L}{nV_t}$$

$$\tau \cdot \frac{Z \cdot \dot{i}_L}{nV_t} = \left(k - 1 - \frac{R_L}{R}\right) \cdot \frac{R}{Z} \cdot \frac{Z \cdot i_L}{nV_t} - \frac{v_C}{nV_t} - \frac{v_{C^*}}{nV_t}$$

$$\tau \cdot e \cdot \frac{\dot{v}_{C^*}}{nV_t} = \frac{Z \cdot I_0}{nV_t} + \frac{Z \cdot i_L}{nV_t} - \frac{Z \cdot I_{DS}}{nV_t} \cdot \left(e^{\frac{v_{C^*}}{nV_t}} - 1\right)$$




```
//time constant and dimensionless parameters
parameter SI.Current I0=Vb/R0 "Estimated supply current";
parameter SI.Time Tau=sqrt(L*C) "Time constant";
parameter SI.Impedance Z=sqrt(L/C) "Characteristic impedance (rho)";
parameter Real k=Z/R*a + 1 + RL/R "Amplification";
parameter Real a=0.95;
parameter Real b=Z*I0/nVt;
parameter Real c=Z*Ids/nVt;
parameter Real e=Cs/C "epsilon";
//components
parameter SI.Resistance R =1.0e3 "Resistor r";
parameter SI.Resistance R1=10.e3 "Resistor r1";
parameter SI.Resistance R2=R1*(k - 1) "Resistor r2 (tunable)";
parameter SI.Resistance R0=20.e3 "Resistor r0";
parameter SI.Voltage Vb=20 "Supply voltage";
parameter SI.Inductance L=100e-3 "Inductor";
parameter SI.Resistance RL=50 "Resistance of Inductor";
parameter SI.Capacitance C =100e-9 "Capacitor c";
parameter SI.Capacitance Cs=15.e-9 "Capacitor c*";
//diode
parameter SI.Current Ids=1e-9 "Diode: saturation current";
parameter SI.Voltage nVt=2*26e-3
"Diode: n * voltage equivalent of temperature";
```

8_Colpitts Oscillator

https://link.springer.com/book/10.1007/978-3-319-05900-6 (1.3)

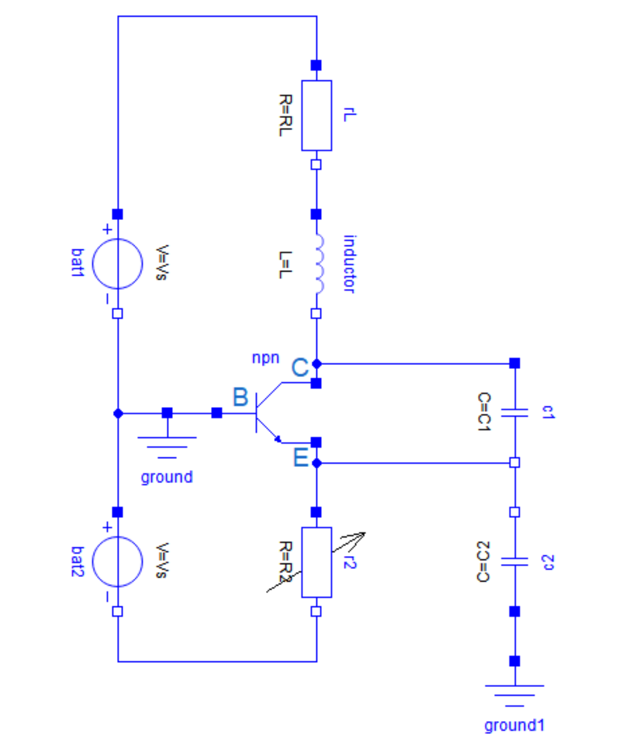
https://ieeexplore.ieee.org/document/331536

$$C_1 \cdot \frac{dv_1}{dt} = i_L - \beta \cdot i_B$$

$$C_2 \cdot \frac{dv_2}{dt} = -\frac{V_{s-} + v_2}{R_2} - i_L - i_B$$

$$L \cdot \frac{di_L}{dt} = V_{s+} - v_1 + v_2 - R_L \cdot i_L$$

$$i_B = \begin{cases} v_2 = v_{BE} \leq V_{th} \rightarrow & 0 \\ v_2 = v_{BE} > V_{th} \rightarrow & \dfrac{v_2 - V_{th}}{R_{on}} \end{cases}$$




```
parameter SI.Resistance RL=35. "Resistance of L";
parameter SI.Inductance L=98.5e-6 "Inductor";
parameter SI.Resistance R2=1000 "Resistor 2";
parameter SI.Capacitance C1=54.e-9 "Capacitor 1";
parameter SI.Capacitance C2=54.e-9 "Capacitor 2";
parameter SI.Voltage Vs=5 "Source Voltage";

parameter SI.Voltage Vth=0.75 "Transistor threshold voltage";
parameter SI.Resistance Ron=100
  "Small-signal on-resistance of base-emitter junction";
parameter Real beta=200 "Transistor forward current gain";
```

9_Shinriki Oscillator

https://pawn.physik.uni-wuerzburg.de/~slueck/PhyAmSa09/Home_files/Examensarbeit_Lueck.pdf

https://ieeexplore.ieee.org/abstract/document/1456241

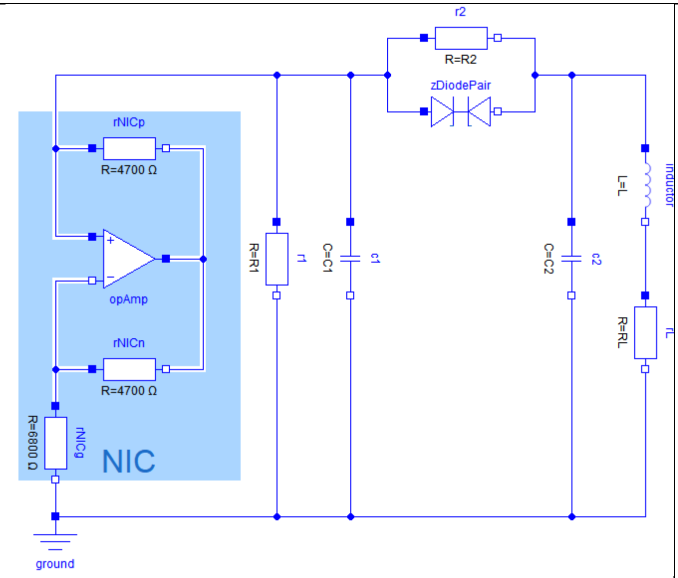
$$i_z = \begin{cases} |v_z| < V_{bt} & 0 \\ |v_z| \geq V_{bt} & sign(v_z) \cdot [a \cdot (|v_z| - V_{bt}) + b \cdot (|v_z| - V_{bt})^3 + c \cdot (|v_z| - V_{bt})^5] \end{cases}$$

$$C_1 \cdot \frac{dv_1}{dt} = -i_{NIC} - \frac{v_1}{R_1} - i_z$$

$$C_2 \cdot \frac{dv_2}{dt} = i_z - i_L$$

$$v_2 = L \cdot \frac{di_L}{dt} + R_L \cdot i_L$$

$$g_{NIC} = \frac{di_{NIC}}{dv_{NIC}} = \begin{cases} |v_{NIC}| > V_{Lim} & g_+ \\ |v_{NIC}| \leq V_{Lim} & g_- \end{cases}$$




```
parameter SI.Inductance L=320e-3 "Inductor";
parameter SI.Resistance RL=100. "Resistor of L";
parameter SI.Resistance R1=60e3 "Resistor 1";
parameter SI.Resistance R2=20e3 "Resistor 2";
parameter SI.Capacitance C1=10.e-9 "Capacitor 1";
parameter SI.Capacitance C2=100e-9 "Capacitor 2";
```

$$V_{bt} = 3.3\ V$$

$$a = 1{,}0862\ \frac{mA}{V}$$

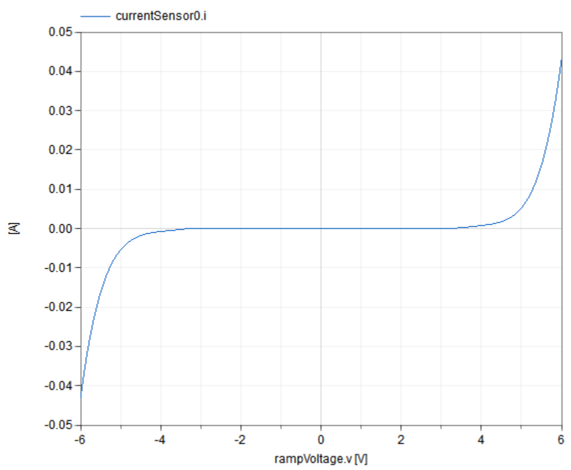
$$b = -0{,}1615\ \frac{mA}{V^3}$$

$$c = 0{,}3021\ \frac{mA}{V^5}$$

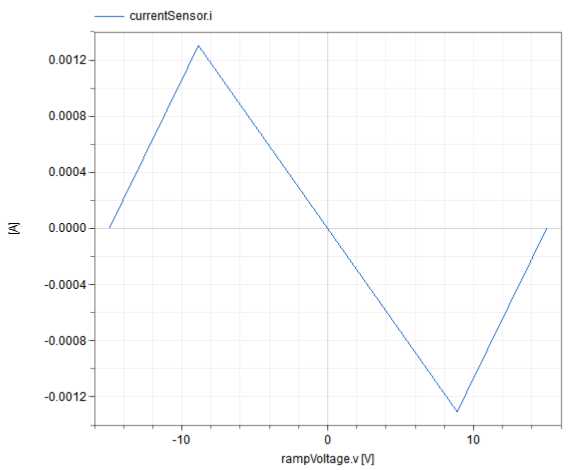
$$V_{Lim} = V_s \cdot \frac{6800}{4700 + 6800}$$

$$g_+ = +\frac{1000}{4700}\ mS$$

$$g_- = -\frac{1000}{6800}\ mS$$



Characteristic of the Zener diode pair



Characteristic of the NIC
(negative impedance converter)

Investigation of the Zener diode pair approximation:

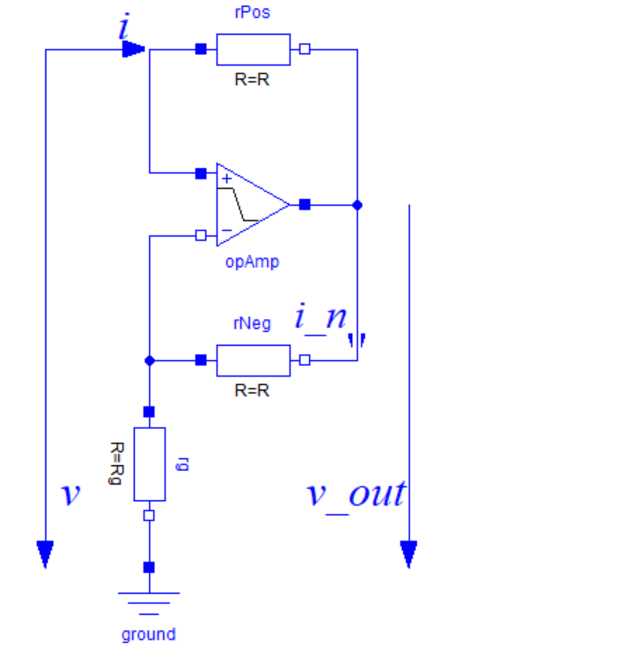
$$i_z = \begin{cases} |v_z| < V_{bt} & 0 \\ |v_z| \geq V_{bt} & sign(v_z) \cdot [a \cdot (|v_z| - V_{bt}) + b \cdot (|v_z| - V_{bt})^3 + c \cdot (|v_z| - V_{bt})^5] \end{cases}$$

$$\frac{di_z}{dv_z} = \begin{cases} |v_z| < V_{bt} & 0 \\ |v_z| \geq V_{bt} & sign(v_z) \cdot [a + 3b \cdot (|v_z| - V_{bt})^2 + 5c \cdot (|v_z| - V_{bt})^4] \end{cases}$$

The first derivative $\frac{di_z}{dv_z}$ is not continuous at $|v_z| = V_{bt}$.

If voltage v is prescribed, the current i can be unambiguously determined.
If current i is prescribed, between $-V_{bt}$ and $+V_{bt}$ there is a manifold of solutions for the voltage v.
For this application, this restriction has no influence.
This restriction could be solved by adaption the approximation, i.e. exchange the horizontal line in the range $-V_{bt} < v_z < +V_{bt}$ against a characteristic with small constant positive slope and adapt the polynomial approximation to achieve a one times continuously differentiable characteristic.

Investigation of the negative impedance converter (NIC):



As long as the opAmp operates in the linear region:

$$i_n = \frac{v_{out} - v}{R} = \frac{v}{R_g} \rightarrow v_{out} = v \cdot \frac{R + R_g}{R_g}$$

$$i = \frac{v - v_{out}}{R} = -\frac{v}{R_g}$$

$$g_- = \frac{1}{R_g}$$

When the opAmp's output saturates:

$$V_{Lim} = V_s \cdot \frac{R_g}{R + R_g}$$

$$v \geq +V_{Lim}: i = \frac{v - V_{Lim}}{R}$$

$$g_+ = \frac{1}{R}$$

If voltage v is prescribed, the current i can be unambiguously determined.
If current i is prescribed, in the range between the zero crossings the voltage v has 3 possible solutions.
For this application, this restriction has no influence.

<u>10_Jerk Circuit</u>

https://link.springer.com/book/10.1007/978-3-319-05900-6 (3.1)

https://sprott.physics.wisc.edu/pubs/paper352.pdf

The name of the system stems from the third derivative of x, which – in a mechanical system – is the derivative of acceleration called jerk.

$$\dddot{x} + A \cdot \ddot{x} + f(\dot{x}) + x = 0$$

$$f(\dot{x}) = R \cdot I_S \cdot \left(e^{\frac{\dot{x}}{nV_t}} - 1 \right)$$

$$\dot{x} = y$$

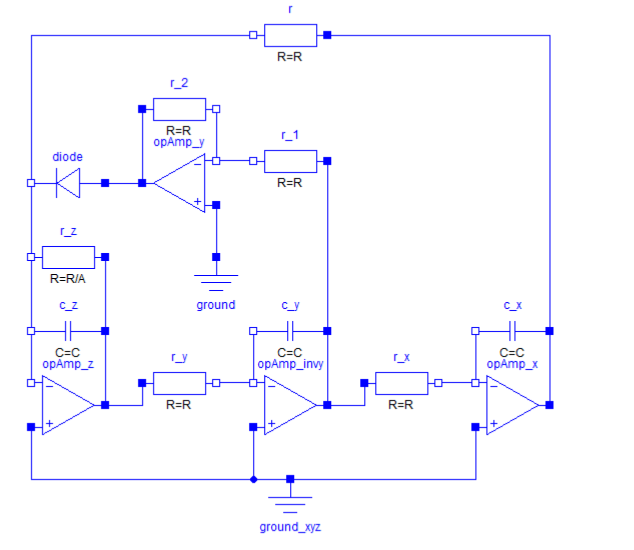
$$\ddot{x} = \dot{y} = z$$

$$\dddot{x} = \ddot{y} = \dot{z}$$

$$\dot{z} = -A \cdot z - x - f(y)$$

The values stay pretty inside a practicable range for a normal voltage supply.

Using 4 operational amplifiers and an acceleration factor of 1000, the circuit can be implemented as follows. The parameter A influences only the feedback resistor at opAMp_z:




```
parameter Real A=0.3 "Parameter to be varied";
parameter SI.Resistance R=1e3 "Resistance";
parameter SI.Capacitance C=1e-6 "Capacitance";
parameter SI.Current Ids=1e-12 "Sat.current";
parameter SI.Voltage nVt=26e-3 " voltage equ.";
```

A=0.3 for periodic results

A=1.0 for chaotic results