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Mechanical
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Developing an Open-Source Frequency Domain Modal Analysis Algorithm in Python

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1 Introduction

1.1 Modal Analysis

In *linear* structural dynamics, *Modal Analysis* is universally recognized as the pre-eminent solution for the identifying and characterizing structures or systems. It achieves this by studying the structure's *modal properties or parameters*—its natural frequencies, mode shapes, and damping ratios. Whether using mathematical modelling or experimental testing, modal analysis is key for engineers to understand the response of structures to various excitations or forces, ensuring safety, compliance with standards and regulations and supporting many research areas such as structural health monitoring or system identification.

Fundamentally, modal analysis is the decomposition of the complex oscillatory behaviour of structures into smaller, more intuitive components called *modes*. Each mode is a mathematical representation of a specific vibration pattern associated with a *natural frequency*, the frequency (or set of) at which a system tends to oscillate when displaced, and a corresponding *mode shape*, a vector which describes the relative movement among the degrees-of-freedom (DOFs) or axis points. The *damping ratio*, a unitless parameter, quantifies the energy dissipation of the system at these natural frequencies. The modal properties are defined by the interaction of the system's physical properties, its mass, stiffness, and damping. These inherent properties guide the system's vibration when subject to external forcing or initial displacements or velocities.

Based on the theory, the standard procedure for modal analysis begins with forming the equations of motion (EOMs) that represent a system, typically, second order matrix differential equations. Consider a system with an arbitrary number N , degrees-of-freedom as shown in figure 1.1. Using Newton's second law,

$$\sum F_i = m_i \ddot{x}_i$$

Where F_i is a force acting on the i -th DOF, m_i is the mass, and x_i is the coordinate, or alternatively the Euler-Lagrange equation as such:

$$\frac{d}{dt} \left(\frac{\partial T}{\partial \dot{q}_i} \right) - \frac{\partial T}{\partial q_i} + \frac{\partial U}{\partial q_i} = Q_i$$

Where q_i is a generalized coordinate (take $q_i = x_i$ for this system), T is the system's kinetic energy, U is the potential energy, and Q_i represents the non-conservative forces. The resulting equations of motion for the system are given in Equation 1.1.

$$\begin{aligned} m_1 \ddot{x}_1 + (c_1 + c_2) \dot{x}_1 - c_2 \dot{x}_2 + (k_1 + k_2) x_1 - k_2 x_2 &= F_1 \\ m_2 \ddot{x}_2 + (c_2 + c_3) \dot{x}_1 - c_2 \dot{x}_1 - c_3 \dot{x}_3 + (k_2 + k_3) x_2 - k_2 x_1 - k_3 x_3 &= F_2 \\ &\dots \\ m_N \ddot{x}_N + (c_N + c_{N+1}) \dot{x}_N - c_{N-1} \dot{x}_{N-1} + (k_N + k_{N+1}) x_N - k_{N-1} x_{N-1} &= F_N \end{aligned} \tag{1.1}$$

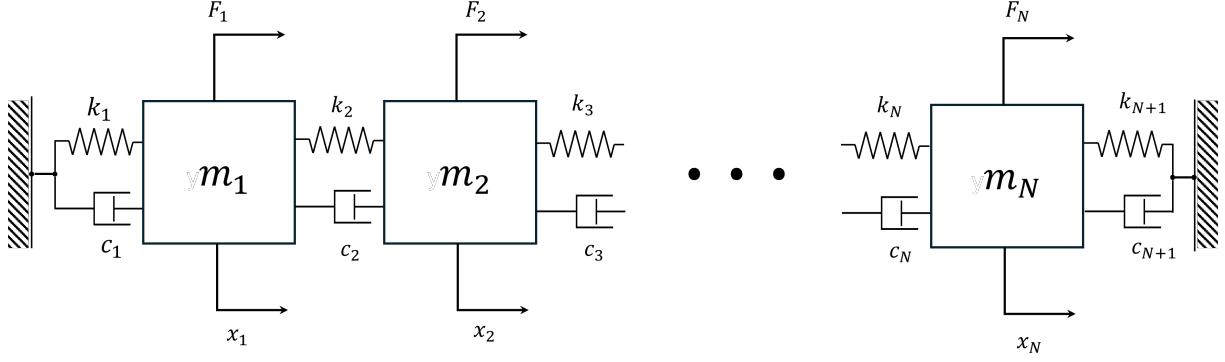


Figure 1.1: A "lumped-mass" system of N degrees-of-freedom

By assembling the physical parameters into respective matrices as highlighted in Equation 1.2, the characteristic differential equation of the system is obtained:

$$[\mathbf{K}] = \begin{bmatrix} k_1 + k_2 & -k_2 & 0 & \dots & 0 \\ -k_2 & k_2 + k_3 & -k_3 & \dots & 0 \\ 0 & -k_3 & k_3 + k_4 & -k_4 & 0 \\ \dots & \dots & \dots & \ddots & \dots \\ 0 & 0 & 0 & -k_N & k_N + k_{N+1} \end{bmatrix} \quad (1.2)$$

$$[\mathbf{C}] = \begin{bmatrix} c_1 + c_2 & -c_2 & 0 & \dots & 0 \\ -c_2 & c_2 + c_3 & -c_3 & \dots & 0 \\ 0 & -c_3 & c_3 + c_4 & -c_4 & 0 \\ \dots & \dots & \dots & \ddots & \dots \\ 0 & 0 & 0 & -c_N & c_N + c_{N+1} \end{bmatrix}$$

$$[\mathbf{M}] = \text{diag}(m_i) \quad \forall i = 1, 2, \dots, N$$

$$\therefore [\mathbf{M}]\ddot{\mathbf{x}} + [\mathbf{C}]\dot{\mathbf{x}} + [\mathbf{K}]\mathbf{x} = \mathbf{F} \quad (1.3)$$

For simplicity, assume the system presented vibrates freely, and is undamped, so \mathbf{F} and $[\mathbf{C}]$ are zero. If the solution of the presented differential equation is harmonic, i.e. $\mathbf{x}(t) = \Psi e^{j\omega t}$, one finds that equation 1.3 reduces to:

$$([\mathbf{K}] - \omega^2[\mathbf{M}])\Psi = 0 \quad (1.4)$$

Rearranging the terms, the equation into takes the general form of an eigenvalue problem:

$$\begin{aligned} [\mathbf{A}] &= [\mathbf{M}]^{-1}[\mathbf{K}] \\ [\mathbf{A}]\Psi &= \omega^2\Psi \end{aligned} \quad (1.5)$$

Here, \mathbf{A} is the so-called dynamical matrix, ω^2 is the eigenvalue — often referred to as an *eigenfrequency* — and Ψ is the corresponding eigenvector representing the mode shape.

In discrete systems, with a finite number of degrees of freedom, the modal analysis is performed using the dynamical matrix $[\mathbf{A}]$, which encapsulates the system's inertial and elastic properties. When extending the approach to continuous systems (systems described by continuous functions), the physical parameters are distributed spatially. This results in a partial differential equation that governs the motion, where finite-dimensional matrices are replaced by linear operators. Consequently, an eigenvalue problem is formed in terms of a differential operator, with eigenvalues corresponding to the natural frequencies* and the

associated eigenfunctions representing the mode shapes in the spatial domain¹. For example this principle applied to transverse vibration of an Euler-Bernoulli beam yields the eigenvalue problem:

$$\Delta^2 Y(x) = \beta^4 Y(x) \quad (1.6)$$

where Δ is the Laplacian operator (i.e. second partial derivative in Cartesian coordinate system), and $\beta^4 = \frac{\omega^2}{c^2}$, in which ω is the natural frequency, and c^2 is the ratio of the beam's flexural rigidity and its inertia.

In both discrete and continuous cases, the process of reducing the governing equations into eigenvalue problems is mathematically elegant, robust, and applicable to all linear systems. Despite this approach's elegance, its practical applications rarely exist. Real world structures and systems seldom conform to the idealized assumptions of lumped-mass systems or Euler-Bernoulli beams with known boundary conditions, this discrepancy can be attributed to more complex geometries, or internal interactions between the components of a system. This limitation has incentivized both academics and practitioners to approach modal analysis differently.

¹An *eigenvector*, or an *eigenfunction*, of a matrix or linear operator defined on some vector/function space is any non-zero vector/function in said space that when multiplied or acted upon by the matrix/linear operator is equivalent to being multiplied by some scalar factor, said scalar factor is referred to as the *eigenvalue*.

Report Story:

Structural Dynamics in engineering

- How studying structural mechanics has helped us have safer, lighter, greener structures.
- Modal Analysis, is regarded as **the** solution for linear structural dynamics.
- Maths of modal analysis:
 - EOM formulation.
 - Eigendecomposition of state matrices.
 - FRF in modal terms. (refer to plscf solution using that)
- This is in various industries, home appliances, aero, civil/structural, acoustics etc.
- Experimental Modal Analysis king.
- Curve-fitting methods for modal analysis.
- The need for algorithms in practice.

Onto software usage in engineering contexts

- engineers consistently rely on software tools, this is great as it streamlines the important processes.
- Important aspects of software dev. :
 - logic/control flow
 - complexities and big O notation
 - unit testing and integration testing.
 - version control.
 - foss vs. prop. discuss why it's cheaper in long run, and better for everyone involved.
- Revisit the aims and objectives.

2 Algorithms / development:

maths-y bit

- lsce (brief)
- lscf (brief)
- plscf (important bits and refer to appendix for full derivation, use own notation and wording).
- Why the companion matrix solution works. $\text{eig}(C(p)) = \lambda_i \rightarrow p(\lambda) = 0$
- here one must explain what poles are for a system.
- lsfd for modeshapes.

software-y bit

- time complexity optimization. discuss that O notation doesn't always equal less time.
- unit testing, explain pytest stuff and fixturing and bla bla bla.
- using numpy (BLAS routines/subroutines)
- user facing code.
- formatting guidelines.

3 Results

- plscf on simulated modal data.
 - clean
 - noisy
 - slightly nonlinear data (mimo where $H_{ij} \approx H_{ji}$ but $H_{ij} \neq H_{ji}$)
 - high dofs.
- plscf on actual lab data.
- adam's plscf vs siemens lms polymax on same dataset.
- interpretation of stabilization diagram.

```
1 import numpy as np
2
3 def _make_polynomial_basis_fcn(
4     polynomial_order: int, frequency_vector: np.ndarray,
5     sampling_frequency: float
6 ) :
7     """Function that creates a Polynomial Basis Function matrix
8
9     Args:
10         polynomial_order (int): Order of the polynomial created.
11             i.e. if 2 then  $P(x) = a_0 * x^0 + a_1 * x^1 + a_2 * x^2$ 
12             in the case of pLSCF,  $\Omega(\omega) = P(e^{j\omega \Delta t})$ 
13
14         frequency_vector (np.ndarray): vector of frequencies
15             measured or simulated, can be hz or rads^-1.
16             MUST be either a row or column vector/1D Array
17
18     Returns:
19         Polynomial basis function matrix.
20
21     """
22     # the polynomial basis function is actually the vandermonde
23     # matrix for the polynomials, A and B.
24     dt = 1 / sampling_frequency # Sampling rate
```

```
20     s = np.exp(1.j*frequency_vector*dt) # this is the "x" in the
        polynomial
21     return np.vander(x=s, N=polynomial_order+1, increasing=True)
```

Consider the Jacobian matrix, for a system with $n_{outputs} = 3$:

$$J = \begin{pmatrix} X_1 & 0 & 0 & Y_1 \\ 0 & X_2 & 0 & Y_2 \\ 0 & 0 & X_3 & Y_3 \end{pmatrix} \quad (3.1)$$

$$J^H J = \begin{pmatrix} X_1^H X_1 & 0 & 0 & X_1^H Y_1 \\ 0 & X_2^H X_2 & 0 & X_2^H Y_2 \\ 0 & 0 & X_3^H X_3 & X_3^H Y_3 \\ X_1^* Y_1^T & X_2^* Y_2^T & X_3^* Y_3^T & Y_1^H Y_1 + Y_2^H Y_2 + Y_3^H Y_3 \end{pmatrix} \quad (3.2)$$

if:

$$R_o = Re(X_o^H X_o)$$

$$S_o = Re(X_o^H Y_o)$$

$$T_o = Re(Y_o^H Y_o)$$

$$2Re(J^H J)\theta = 2Re \begin{pmatrix} X_1^H X_1 & 0 & 0 & X_1^H Y_1 \\ 0 & X_2^H X_2 & 0 & X_2^H Y_2 \\ 0 & 0 & X_3^H X_3 & X_3^H Y_3 \\ X_1^* Y_1^T & X_2^* Y_2^T & X_3^* Y_3^T & Y_1^H Y_1 + Y_2^H Y_2 + Y_3^H Y_3 \end{pmatrix} \begin{pmatrix} \beta_1 \\ \beta_2 \\ \beta_3 \\ \alpha \end{pmatrix} \quad (3.3)$$

$$= 2 \begin{pmatrix} R_1\beta_1 + S_1\alpha \\ R_2\beta_2 + S_2\alpha \\ R_3\beta_3 + S_3\alpha \\ S_1^T\beta_1 + S_2^T\beta_2 + S_3^T\beta_3 + (T_1 + T_2 + T_3)\alpha \end{pmatrix} \quad (3.4)$$

which corresponds to the solutions in the normal equations in terms of alpha and beta.

$$l^{LS}(\theta) = \text{tr}\{\theta^T Re(J^H J)\theta\} \quad (3.5)$$

from vector calculus, if

$$\mathbf{f} = \mathbf{x}^T \mathbf{B} \mathbf{x} \quad (3.6)$$

then,

$$\frac{\partial \mathbf{f}}{\partial \mathbf{x}} = 2\mathbf{B} \mathbf{x} \quad (3.7)$$

then the normal equation for polymax should be:

$$\frac{\partial l^{LS}}{\partial \theta} = 2Re(J^H J)\theta \quad (3.8)$$

A Derivation of p-LSCF modal parameter estimation method

A.1 The right-matrix rational fractional model

The polyreference least-squares complex frequency domain method employs a right matrix fractional model to fit MIMO Frequency Response Function measurements into a set of rational polynomial transfer functions:

$$[H(\omega)] = [N(\omega)][D(\omega)]^{-1} \quad (\text{A.1})$$

Such that $H(\omega) \in \mathbb{C}^{N_{outputs} \times N_{inputs}}$ is the FRF matrix, where $D(\omega) \in \mathbb{C}^{N_{inputs} \times N_{inputs}}$, is the denominator matrix polynomial, and $N(\omega) \in \mathbb{C}^{N_{outputs} \times N_{inputs}}$, is the numerator matrix polynomial. The rows corresponding to each output o in the FRF matrix can be represented as such:

$$\langle H_o(\omega) \rangle = \langle N_o(\omega) \rangle [D(\omega)]^{-1} \quad (\text{A.2})$$

The row vector numerator polynomial for the o^{th} output, and the denominator matrix polynomial are defined in terms of a polynomial basis function, $\Omega(\omega)$, and their respective polynomial coefficients, β and α as such:

$$\langle N_o(\omega) \rangle = \sum_{r=1}^p \Omega_r(\omega) \langle \beta_{or}(\omega) \rangle \quad (\text{A.3})$$

$$[D(\omega)] = \sum_{r=1}^p \Omega_r(\omega) [\alpha_r] \quad (\text{A.4})$$

With the polynomial basis function $\Omega_r(\omega) = e^{j\omega\Delta t r}$. Although not initially obvious as polynomials with conventional form $p(x) = c_0 + c_1x + c_2x^2 + \dots + c_nx^n$, the basis functions are expressed in the s -domain where $s = e^{j\omega\Delta t}$. The polynomial coefficients, $\alpha_r \in \mathbb{R}^{N_{inputs} \times N_{inputs}}$ and $\beta_{or} \in \mathbb{R}^{1 \times N_{inputs}}$, are assembled into matrix form:

$$\beta_o = \begin{pmatrix} \beta_{o0} \\ \beta_{o1} \\ \beta_{o2} \\ \dots \\ \beta_{op} \end{pmatrix} \in \mathbb{R}^{(p+1) \times N_{inputs}} \quad (\text{A.5})$$

$$\alpha = \begin{pmatrix} \alpha_0 \\ \alpha_1 \\ \alpha_2 \\ \dots \\ \alpha_p \end{pmatrix} \in \mathbb{R}^{N_{inputs} * (p+1) \times N_{inputs}} \quad (\text{A.6})$$

$$\theta = \begin{pmatrix} \beta_0 \\ \beta_1 \\ \beta_2 \\ \dots \\ \beta_{N_o} \\ \alpha \end{pmatrix} \in \mathbb{R}^{(N_{outputs} + N_{inputs})(p+1) \times N_{inputs}} \quad (\text{A.7})$$

A.2 Minimizing the sum of the squared residuals

The collection of both sets of coefficients into one variable θ , makes performing the least squares problem simpler, in a sense, as it becomes the one unknown in this least squares model. As typical in any fitting method, one must minimize the error between the model and the real or measured value. The nonlinear least-squares error for:

Measured FRF: $\hat{H}_o(\omega_k)$

Model FRF: $H_o(\omega_k)$

is weighted such that:

$$\epsilon_o^{NLS}(\theta, \omega_k) = w_o(\omega_k)(H_o(\omega_k) - \hat{H}_o(\omega_k)) \quad (\text{A.8})$$

Where $\epsilon_o^{NLS} \in \mathbb{C}^{1 \times N_{inputs}}$, $w_o(\omega_k)$ is a scalar weighing function which captures the variation and deviation between multiple inputs on the same measurement point, and $\forall k = 0, 1, 2, \dots, N_{frequency}$. Said weighing function is typically denoted by

$$w_o(\omega_k) = \frac{1}{\sqrt{\text{var}[H_o(\omega_k)]}} \quad (\text{A.9})$$

(See [reference for weighted linear regressions] for more information on weighted least squares.) One can then define the nonlinear cost function as the sum of the error "squared", (hermitian inner product), over the data points, in this case, spectral lines and outputs;

$$l^{NLS}(\theta) = \sum_{o=1}^{N_{out}} \sum_{k=1}^{N_f} \text{tr}\{(\epsilon_o^{NLS}(\theta, \omega_k))^H \epsilon_o^{NLS}(\theta, \omega_k)\} \quad (\text{A.10})$$

In this equation, $\text{tr}\{\bullet\}$ denotes the trace of a matrix, also known as the sum of diagonal elements, and \bullet^H denotes the Hermitian (conjugate) transpose. The trace operator is used as the trace of a product of 2 matrices $\mathbf{A} \in \mathbb{C}^{m \times n}$ and $\mathbf{B} \in \mathbb{C}^{n \times m}$ will equal the sum of each individual element in \mathbf{A} with the individual elements of \mathbf{B} . This provides a sum of all square residuals/errors in the cost function.

$$\text{tr}\{\mathbf{A}^H \mathbf{B}\} = \text{tr}\{\mathbf{A} \mathbf{B}^H\} = \text{tr}\{\mathbf{B}^H \mathbf{A}\} = \text{tr}\{\mathbf{B} \mathbf{A}^H\} = \sum_{i=1}^m \sum_{j=1}^n a_{ij} b_{ij} \quad (\text{A.11})$$

A.3 Linearizing the error

One can then obtain the polynomial coefficients through minimizing the cost function in A.10, by setting the derivative $\frac{\partial l^{NLS}}{\partial \theta}$ equal to zero, however a nonlinear cost function will yield nonlinear derivative equations, (typically called normal equations in linear regression). A subsequent linearization of the cost function can approximate (suboptimally) the least squares problem, this is achieved through right multiplying the cost function with denominator polynomial \mathbf{D} . This gives a linear error:

$$\begin{aligned} \epsilon_o^{LS}(\omega_k, \theta) &= w_o(\omega_k)(N_o(\omega_k, \beta_o) - \hat{H}_o(\omega_k)D(\omega_k, \alpha)) \\ &= w_o(\omega_k) \sum_{r=0}^p (\Omega_r(\omega_k)\beta_{or} - \Omega_r(\omega_k)\hat{H}_o(\omega_k)\alpha_r) \end{aligned} \quad (\text{A.12})$$

Stacking the error in terms for all spectral lines in one matrix $E_o^{LS}(\theta) \in \mathbb{C}^{N_f \times N_i n}$:

$$E_o^{LS}(\theta) = \begin{pmatrix} \epsilon_o^{LS}(\omega_1, \theta) \\ \epsilon_o^{LS}(\omega_2, \theta) \\ \epsilon_o^{LS}(\omega_3, \theta) \\ \vdots \\ \epsilon_o^{LS}(\omega_{N_f}, \theta) \end{pmatrix} = \begin{pmatrix} X_o & Y_o \end{pmatrix} \begin{pmatrix} \beta_o \\ \alpha \end{pmatrix} \quad (\text{A.13})$$

Here, new variables \mathbf{X} and \mathbf{Y} are introduced:

$$X_o = \begin{pmatrix} w_o(\omega_1) \left(\Omega_0(\omega_1) + \Omega_1(\omega_1) \dots \Omega_p(\omega_1) \right) \\ w_o(\omega_2) \left(\Omega_0(\omega_2) + \Omega_1(\omega_2) \dots \Omega_p(\omega_2) \right) \\ \vdots \\ w_o(\omega_{N_f}) \left(\Omega_0(\omega_{N_f}) + \Omega_1(\omega_{N_f}) \dots \Omega_p(\omega_{N_f}) \right) \end{pmatrix} \in \mathbb{C}^{N_f \times (p+1)} \quad (\text{A.14})$$

$$Y_o = \begin{pmatrix} -w_o(\omega_1) \left(\Omega_0(\omega_1) + \Omega_1(\omega_1) \dots \Omega_p(\omega_1) \right) \otimes \hat{H}_o(\omega_1) \\ -w_o(\omega_2) \left(\Omega_0(\omega_2) + \Omega_1(\omega_2) \dots \Omega_p(\omega_2) \right) \otimes \hat{H}_o(\omega_2) \\ \vdots \\ -w_o(\omega_{N_f}) \left(\Omega_0(\omega_{N_f}) + \Omega_1(\omega_{N_f}) \dots \Omega_p(\omega_{N_f}) \right) \otimes \hat{H}_o(\omega_{N_f}) \end{pmatrix} \in \mathbb{C}^{N_f \times N_{in}(p+1)} \quad (\text{A.15})$$

Where \otimes is the Kronecker product. In these equations, \mathbf{X} is used to capture the frequency content of the least squares problem, and \mathbf{Y} is used to capture both the frequency content and the measured response data. Using these matrices, one can reconstruct the nonlinear cost function into one that is linear:

$$\begin{aligned} l^{LS}(\theta) &= \sum_{o=1}^{N_{out}} \sum_{k=1}^{N_f} \mathbf{tr}\{(\epsilon_o^{LS}(\omega_k, \theta))^H \epsilon_o^{LS}(\omega_k, \theta)\} \\ &= \sum_{o=1}^{N_{out}} \mathbf{tr}\{(E_o^{LS}(\theta))^H E_o^{LS}(\theta)\} \\ &= \sum_{o=1}^{N_{out}} \mathbf{tr}\left\{\begin{pmatrix} \beta_o^T & \alpha^T \end{pmatrix} \begin{pmatrix} X_o^H \\ Y_o^H \end{pmatrix} (X_o \quad Y_o) \begin{pmatrix} \beta_o \\ \alpha \end{pmatrix}\right\} \end{aligned} \quad (\text{A.16})$$

If one defines a *Jacobian* matrix $\mathbf{J} \in \mathbb{C}^{N_f N_{out} \times (N_{in} + N_{out})(p+1)}$ for the problem as such:

$$\mathbf{J} = \begin{pmatrix} X_1 & 0 & \dots & 0 & Y_1 \\ 0 & X_2 & \dots & 0 & Y_2 \\ \dots & \dots & \dots & \dots & \dots \\ 0 & 0 & 0 & X_{N_{out}} & Y_{N_{out}} \end{pmatrix} \quad (\text{A.17})$$

The cost function can be represented as:

$$l^{LS}(\theta) = \mathbf{tr}\{\theta^T \mathbf{J}^H \mathbf{J} \theta\} \quad (\text{A.18})$$

To obtain real values of θ , one must place a constraint on the cost function such that:

$$l^{LS}(\theta) = \mathbf{tr}\{\theta^T \operatorname{Re}(\mathbf{J}^H \mathbf{J}) \theta\} \quad (\text{A.19})$$

Where the Gramian matrix of \mathbf{J} can be represented in terms a set of variables, \mathbf{R}, \mathbf{S} and \mathbf{T} :

$$\operatorname{Re}(\mathbf{J}^H \mathbf{J}) = \begin{pmatrix} R_1 & 0 & \dots & 0 & S_1 \\ 0 & 0 & \dots & 0 & S_2 \\ \dots & \dots & \dots & \dots & \dots \\ 0 & 0 & \dots & R_{N_{out}} & S_{N_{out}} \\ S_1^T & S_2^T & \dots & S_{N_{out}}^T & \sum_{o=1}^{N_{out}} T_o \end{pmatrix} \quad (\text{A.20})$$

in which:

$$R_o = \text{Re}(X_o^H X_o) \quad (\text{A.21})$$

$$S_o = \text{Re}(X_o^H Y_o) \quad (\text{A.22})$$

$$T_o = \text{Re}(Y_o^H Y_o) \quad (\text{A.23})$$

A.4 The Normal Equations, and extracting the modal parameters

The cost function can then be minimized in terms of α and β to find the best least-squares fit:

$$\frac{\partial l^{LS}(\theta)}{\partial \beta_o} = 2(R_o \beta_o + S_o \alpha) = 0 \quad (\text{A.24})$$

$$\forall O = 1, 2, \dots, N_{out}$$

$$\frac{\partial l^{LS}(\theta)}{\partial \alpha} = 2 \sum_{o=1}^{N_{out}} (S_o^T \beta_o + T_o \alpha) \quad (\text{A.25})$$

Giving normal equations of this least squares problem in terms of the wanted polynomial coefficients, one can also assemble those normal equations into 1 equation:

$$\frac{\partial l^{LS}(\theta)}{\partial \theta} = 2\text{Re}(\mathbf{J}^H \mathbf{J})\theta = 0 \quad (\text{A.26})$$

The denominator coefficients α are used to obtain the poles and the modal participation factors, which are sufficient information for the constructing a stabilization diagram. Hence, one can further reduce the normal equations by setting:

$$\beta_o = R_o^{-1} S_o \alpha \quad (\text{A.27})$$

This yields the reduced normal equation:

$$\left\{ 2 \sum_{o=1}^{N_{out}} (T_o - S_o^T R_o^{-1} S_o) \right\} \alpha = 0 \quad (\text{A.28})$$

$$\mathbf{M}\alpha = 0$$

For a non-trivial solution to the normal equation, a constraint is set on α , where:

$$\alpha_p = \mathbf{I}_{N_{in}} \quad (\text{A.29})$$

The rest of the denominator coefficients are then found using:

$$\mathbf{M}(1 : N_{in} * p, 1 : N_{in} * p) \begin{pmatrix} \alpha_0 \\ \alpha_1 \\ \alpha_2 \\ \vdots \\ \alpha_{p-1} \end{pmatrix} = \mathbf{M}(1 : N_{in} * p, N_{in} * p + 1 : N_{in} * (p + 1)) \quad (\text{A.30})$$

The least-squares estimate for α is then:

$$\hat{\alpha}_{LS} = \left\{ \alpha \middle| \mathbf{I}_{N_{in}} \right\}$$

This makes the denominator polynomial \mathbf{D} a *monic* polynomial. Based on the fundamental definition of system poles, which is the points at which the system's response is "infinite", one can say that for an arbitrary rational polynomial $p(x)$:

$$p(x) = \frac{a_0 + a_1x + a_2x^2 + \cdots + a_nx^n}{b_0 + b_1x + b_2x^2 + \cdots + b_nx^n} \quad (\text{A.31})$$

To achieve said "infinite" value, one must find values of x that represent the roots of the denominator polynomial. In the pLSCF model, one can exploit the monic property of the denominator polynomial. Frobenius companion matrices are square matrices that represent monic polynomials, given one has a monic polynomial

$$p(x) = x^n + a_{n-1}x^{n-1} + a_{n-2}x^{n-2} + \cdots + a_1x + a_0$$

The companion matrix of said polynomial is defined as:

$$C(p) = \begin{bmatrix} 0 & 0 & \dots & 0 & -a_0 \\ 1 & 0 & \dots & 0 & -a_1 \\ 0 & 1 & \dots & 0 & -a_2 \\ \vdots & \vdots & \ddots & \vdots & \vdots \\ 0 & 0 & \dots & 1 & -a_{n-1} \end{bmatrix} \quad (\text{A.32})$$

A property of the companion matrix $C(p) \in \mathbb{R}^{n \times n}$ is that its eigenvalues $\lambda_1, \lambda_2, \dots, \lambda_n$ are the roots of $p(x)$, where $p(\lambda_i) = 0, \forall i = 1, 2, \dots, n$. This property aids in finding the system poles, after constructing the companion matrix for the denominator polynomial, an Eigendecomposition of the matrix yields the discrete time poles as the eigenvalues, and the corresponding eigenvectors are the modal participation factors:

$$C(\mathbf{D}) = \begin{pmatrix} 0 & I & \dots & 0 & 0 \\ 0 & 0 & I & \dots & 0 \\ \dots & \dots & \dots & \dots & \dots \\ 0 & 0 & \dots & 0 & I \\ -\alpha_0^T & -\alpha_1^T & -\alpha_2^T & \cdots -\alpha_{p-2}^T & -\alpha_{p-1}^T \end{pmatrix} \quad (\text{A.33})$$

$$C(\mathbf{D})[\mathbf{L}] = \Lambda[\mathbf{L}] \quad (\text{A.34})$$

Where the matrix $[\mathbf{L}]$ is the Eigenmatrix (matrix with columns as eigenvectors), representing the modal participation factors of each mode, and the matrix Λ contains the discrete time poles on its diagonal elements. The transpose of a companion matrix, this however does not affect the numerical value of the poles or participation factors [reference proof]. A p -order right matrix-fraction polynomial estimation should yield pN_{in} number of poles.

A.5 Finding the modeshapes using the Least-Squares Frequency Domain (LSFD) method

This part should be in actual report: When fitting theoretical models to experimental data, the difficulty does not typically lie in the mathematical framework enabling the modelling process. Instead, the challenge is in constructing a model that provides physically meaningful insights. Given that the goal of many modal parameter estimation methods is to find a set of poles which As apparent, it is straightforward to find the polynomial coefficients using measured data.