



Synchrosqueezed wavelet transforms: An empirical mode decomposition-like tool

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ABSTRACT

The EMD algorithm is a technique that aims to decompose into their building blocks functions that are the superposition of a (reasonably) small number of components, well separated in the time–frequency plane, each of which can be viewed as approximately harmonic locally, with slowly varying amplitudes and frequencies. The EMD has already shown its usefulness in a wide range of applications including meteorology, structural stability analysis, medical studies. On the other hand, the EMD algorithm contains heuristic and ad hoc elements that make it hard to analyze mathematically.

In this paper we describe a method that captures the flavor and philosophy of the EMD approach, albeit using a different approach in constructing the components. The proposed method is a combination of wavelet analysis and reallocation method. We introduce a precise mathematical definition for a class of functions that can be viewed as a superposition of a reasonably small number of approximately harmonic components, and we prove that our method does indeed succeed in decomposing arbitrary functions in this class. We provide several examples, for simulated as well as real data.

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1. Introduction

Time-frequency representations provide a powerful tool for the analysis of time series signals. They can give insight into the complex structure of a “multi-layered” signal consisting of several components, such as the different phonemes in a speech utterance, or a sonar signal and its delayed echo. There exist many types of time-frequency (TF) analysis algorithms; the overwhelming majority belong to either “linear” or “quadratic” methods [1].

In “linear” methods, the signal to be analyzed is characterized by its inner products with (or correlations with) a pre-assigned family of templates, generated from one (or a few) basic template by simple operations. Examples are the windowed Fourier transform, where the family of templates is generated by translating and modulating a basic window function, or the wavelet transform, where the templates are obtained by translating and dilating the basic (or “mother”) wavelet. Many linear methods, including the windowed Fourier transform and the wavelet transform, make it possible to reconstruct the signal from the inner products with templates; this reconstruction can be for the whole signal, or for parts of the signal; in the latter case, one typically restricts the reconstruction procedure to a subset of the TF plane. However, in all these methods, the family of template functions used in the method unavoidably “colors” the representation, and can influence the interpretation given on “reading” the TF representation in order to deduce properties of the signal. Moreover, the Heisenberg uncertainty principle limits the resolution that can be attained in the TF plane; different trade-offs can be achieved by the choice of the linear transform or the generator(s) for the family of templates, but none is ideal, as illustrated

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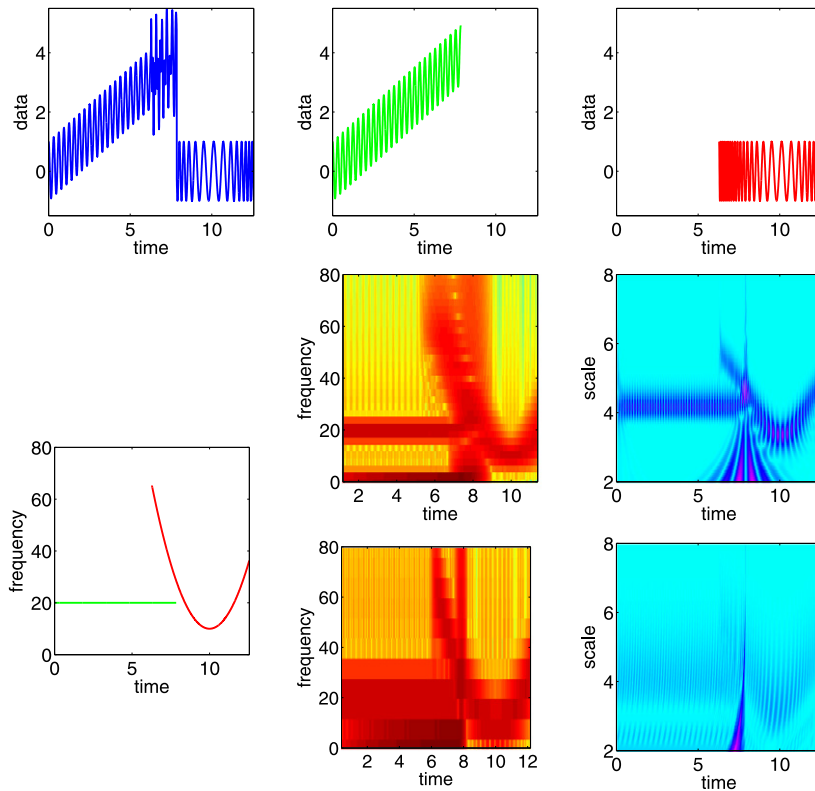


Fig. 1. Examples of linear time-frequency representations. Top row: the signal $s(t) = s_1(t) + s_2(t)$ (top left) defined by $s_1(t) = 0.5t + \cos(20t)$ for $0 \leq t \leq 5\pi/2$ (top middle) and $s_2(t) = \cos(\frac{4}{3}[(t-10)^3 - (2\pi-10)^3] + 10(t-2\pi))$ for $2\pi \leq t \leq 4\pi$ (top right). Next row: left: the instantaneous frequency for its two components (left) $\omega(t) = 20$ for $0 \leq (t-10)^2 \leq 5\pi/2$, and $\omega(t) = 4t^2 + 10$ for $2\pi \leq t \leq 4\pi$; middle: two examples of (the absolute value of) a continuous windowed Fourier transform of $s(t)$, with a wide window ($2\pi/5$) (top) and a narrow window ($\pi/10$) (bottom) [these are plotted with Matlab, with the 'jet' colormap; red indicates higher amplitude]; right: two examples of a continuous wavelet transform of $s(t)$, with a Morlet wavelet (top) and a Haar wavelet (bottom) [plotted with 'hsv' colormap in Matlab; purple indicates higher amplitude]. The instantaneous frequency profile can be clearly recognized in each of these linear TF representations, but it is “blurred” in each case, in different ways that depend on the choice of the transform. (For interpretation of colors in this figure, the reader is referred to the web version of this article.)

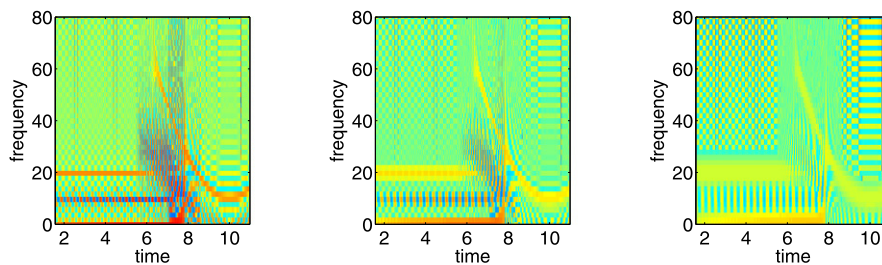


Fig. 2. Examples of quadratic time-frequency representations. Left: the Wigner–Ville transform of $s(t)$, in which interference causes the typical Moiré patterns; middle and right: two pseudo-Wigner–Ville transforms of $s(t)$, obtained by blurring the Wigner–Ville transform slightly using Gaussian smoothing (middle) and somewhat more (right). [All three graphs plotted with ‘jet’ colormap in Matlab, calibrated identically.] The blurring removes the interference patterns, at the cost of precise location in the time–frequency localization.

in Fig. 1. In “quadratic” methods to build a TF representation, one can avoid introducing a family of templates with which the signal is “compared” or “measured”. As a result, some features can have a crisper, “more focused” representation in the TF plane with quadratic methods (see Fig. 2). However, in this case, “reading” the TF representation of a multi-component signal is rendered more complicated by the presence of interference terms between the TF representations of the individual components; these interference effects also cause the “time–frequency density” to be negative in some parts of the TF plane. These negative parts can be removed by some further processing of the representation [1], at the cost of reintroducing some blur in the TF plane. Reconstruction of the signal, or part of the signal, is much less straightforward for quadratic than for linear TF representations.

In many practical applications, in a wide range of fields (including, e.g., medicine and engineering) one is faced with signals that have several components, all reasonably well localized in TF space, at different locations. The components

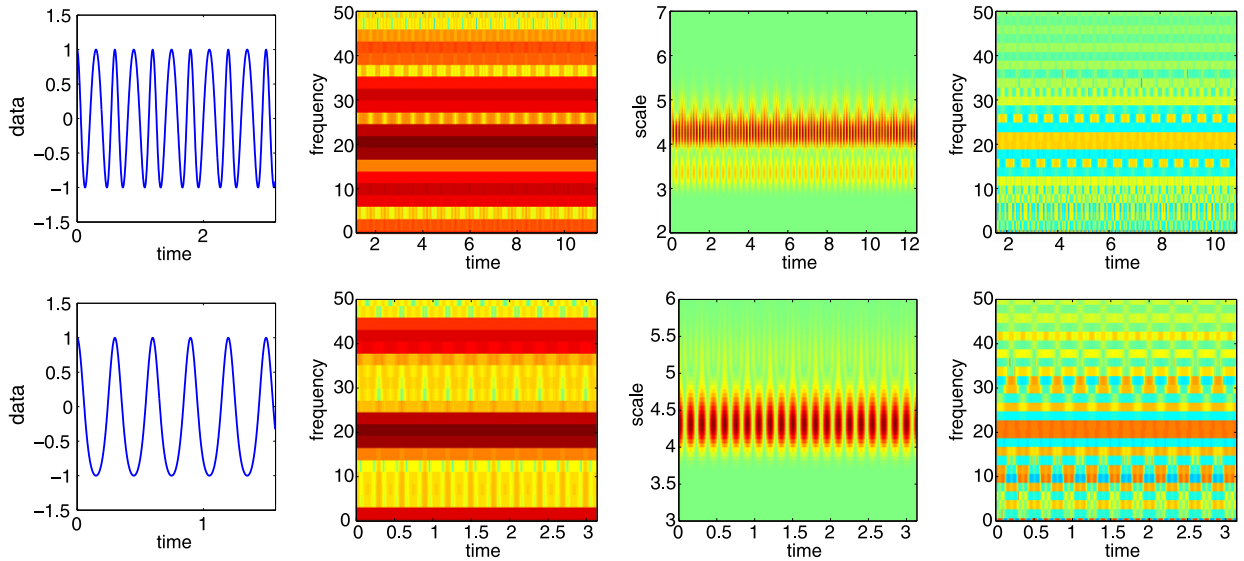


Fig. 3. Two examples of wave functions of the type $\cos[\phi(t)]$, with slowly varying $A(t)$ and $\phi'(t)$, for which standard TF representations are not very well localized in the time–frequency plane. Left: signal; middle left: windowed Fourier transform; middle right: Morlet wavelet transform; right: Wigner–Ville function. [All TF representations plotted with ‘jet’ colormap in Matlab.]

are often also called “non-stationary”, in the sense that they can present jumps or changes in behavior, which it may be important to capture as accurately as possible. For such signals both the linear and quadratic methods come up short. Quadratic methods obscure the TF representation with interference terms; even if these could be dealt with, reconstruction of the individual components would still be an additional problem. Linear methods are too rigid, or provide too blurred a picture. Figs. 1, 2 show the artifacts that can arise in linear or quadratic TF representations when one of the components suddenly stops or starts. Fig. 3 shows examples of components that are non-harmonic, but otherwise perfectly reasonable as candidates for a single-component-signal, yet not well represented by standard TF methods, as illustrated by the lack of concentration in the time–frequency plane of the transforms of these signals. The *Empirical Mode Decomposition* (EMD) method was proposed by Norden Huang [2] as an algorithm that would allow time–frequency analysis of such multi-component signals, without the weaknesses sketched above, overcoming in particular artificial spectrum spread caused by sudden changes. Given a signal $s(t)$, the method decomposes it into several *intrinsic mode functions* (IMF):

$$s(t) = \sum_{k=1}^K s_k(t), \quad (1.1)$$

where each IMF is basically a function oscillating around 0, albeit not necessarily with constant frequency:

$$s_k(t) = A_k(t) \cos(\phi_k(t)), \quad \text{with } A_k(t), \phi'_k(t) > 0 \forall t. \quad (1.2)$$

(Here, and throughout the paper, we use “prime” to denote the derivative, i.e. $g'(t) = \frac{dg}{dt}(t)$.) Essentially, each IMF is an amplitude modulated–frequency modulated (AM–FM) signal; typically, the change in time of $A_k(t)$ and $\phi'_k(t)$ is much slower than the change of $\phi_k(t)$ itself, which means that locally (i.e. in a time interval $[t - \delta, t + \delta]$, with $\delta \approx 2\pi[\phi'_k(t)]^{-1}$) the component $s_k(t)$ can be regarded as a harmonic signal with amplitude $A_k(t)$ and frequency $\phi'_k(t)$. (Note that this differs from the definition given by Huang; in e.g. [2], the conditions on an IMF are phrased as follows: (1) in the whole data set, the number of extrema and the number of zero crossings of $s_k(t)$ must either be equal or differ at most by one; and (2) at any t , the value of a smooth envelope defined by the local minima of the IMF is the negative of the corresponding envelope defined by the local maxima. Functions satisfying (1.2) have these properties, but the reverse inclusion doesn’t hold. In practice, the examples given in [2] and elsewhere typically do satisfy (1.2), however.) After the decomposition of $s(t)$ into its IMF components, the EMD algorithm proceeds to the computation of the “instantaneous frequency” of each component. Theoretically, this is given by $\omega_k(t) := \phi'_k(t)$; in practice, rather than a (very unstable) differentiation of the estimated $\phi_k(t)$, the originally proposed EMD method used the Hilbert transform of the $s_k(t)$ [2]; more recently, this has been replaced by other methods [3].

It is clear that the classes of functions that can be written in the form (1.1) with each component as in (1.2) is quite large. In particular, if $s(t)$ is defined (or observed) in $[-T, T]$ with finite number terms in the Fourier series, then the Fourier series on $[-T, T]$ of $s(t)$ is such a decomposition. It is also easy to see that such a decomposition is far from unique. This is simply illustrated by considering the following signal:

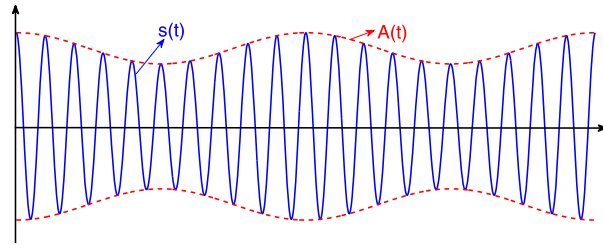


Fig. 4. Non-uniqueness for decomposition into IMT. This function can be considered as a single component, of the type $A(t)\cos[\Omega t]$, with slowly varying amplitude, or as the sum of three components. (See text.)

$$\begin{aligned} s(t) &= 0.25 \cos([\Omega - \gamma]t) + 2.5 \cos(\Omega t) + 0.25 \cos([\Omega + \gamma]t) \\ &= \left(2 + \cos^2 \left[\frac{\gamma}{2} t \right] \right) \cos(\Omega t), \end{aligned} \quad (1.3)$$

where $\Omega \gg \gamma$, so that one can set $A(t) := 2 + \cos^2[\frac{\gamma}{2}t]$, which varies much more slowly than $\cos[\phi(t)] = \cos[\Omega t]$. There are two natural interpretations for this signal: it can be regarded either as a summation of three cosines with frequencies $\Omega - \gamma$, Ω and $\Omega + \gamma$ respectively, or as a single component with frequency Ω and a slowly modulated amplitude. Depending on the circumstances, either interpretation can be the “best”. In the EMD framework, the second interpretation (single component, with slowly varying amplitude) is preferred when $\Omega \gg \gamma$. (See Fig. 4.) The EMD is typically applied when it is more “physically meaningful” to decompose a signal into *fewer* components if this can be achieved by mild variations in frequency and amplitude; in those circumstances, this preference is sensible. Nevertheless, this (toy) example illustrates that we should not expect a universal solution to all TF decomposition problems. For certain classes of functions, consisting of a (reasonably) small number of components, well separated in the TF plane, each of which can be viewed as approximately harmonic locally, with slowly varying amplitudes and frequencies, it is clear, however, that a technique that identifies these components accurately, even in the presence of noise, has great potential for a wide range of applications. Such a decomposition should be able to accommodate such mild variations within the building blocks of the decomposition.

The EMD algorithm, first proposed in [2], made more robust as well as more versatile by the extension in [3] (allowing e.g. applications to higher dimensions), is such a technique. It has already shown its usefulness in a wide range of applications including meteorology, structural stability analysis, medical studies – see, e.g. [4,5,2]; a recent review is given in [6]. On the other hand, the EMD algorithm contains a number of heuristic and ad hoc elements that make it hard to analyze mathematically its guarantees of accuracy or the limitations of its applicability. For instance, the EMD algorithm uses a *sifting process* to construct the decomposition of type (1.1). In each step in this sifting process, two smooth interpolating functions are constructed (using cubic splines), one interpolating the local maxima ($\bar{s}(t)$), the other the local minima ($\underline{s}(t)$). The mean of these two envelopes, $m(t) = (\bar{s}(t) + \underline{s}(t))/2$, is then subtracted from the signal: $r_1(t) = s(t) - m(t)$. This is the first “candidate” for the IMF with highest instantaneous frequency. In most cases, r_1 is not yet a satisfactory IMF; the process is then repeated on r_1 again, etc., thus generating successively better candidates for this IMF; this repeated process is called “sifting”. Sifting is done for either a fixed number of times, or until a certain stopping criterium is satisfied; the final remainder $r_n(t)$ is taken as the first IMF, $s_1 := r_n$. The algorithm continues with the difference between the original signal and the first IMF to extract the second IMF (which is the first IMF obtained from the “new starting signal” $s(t) - s_1(t)$) and so on. (Examples of the decomposition will be given in Section 5.) Because the sifting process relies heavily on interpolates of maxima and minima, the end result has some stability problems in the presence of noise, as illustrated in [7]. The solution proposed in [7], a procedure called EEMD, addresses these issues in practice, but poses new challenges to our mathematical understanding.

Attempts at a mathematical understanding of the approach and the results produced by the EMD method have been mostly exploratory. A systematic investigation of the performance of EMD acting on white noise was carried out in [8,9]; it suggests that in some limit, EMD on signals that don’t have structure (like white noise) produces a result akin to wavelet analysis. The decomposition of signals that are superpositions of a few cosines was studied in [10], with interesting results. A first different type of study, more aimed at building a mathematical framework, is given in [11,12], which analyzes mathematically the limit of an infinite number of “sifting” operations, showing it defines a bounded operator on ℓ_∞ , and studies its mathematical properties.

In summary, the EMD algorithm has shown its usefulness in various applications, yet our mathematical understanding of it is still very sketchy. In this paper we discuss a method that captures the flavor and philosophy of the EMD approach, without necessarily using the same approach in constructing the components. We hope this approach will provide new insights in understanding what makes EMD work, when it can be expected to work (and when not) and what type of precision we can expect.

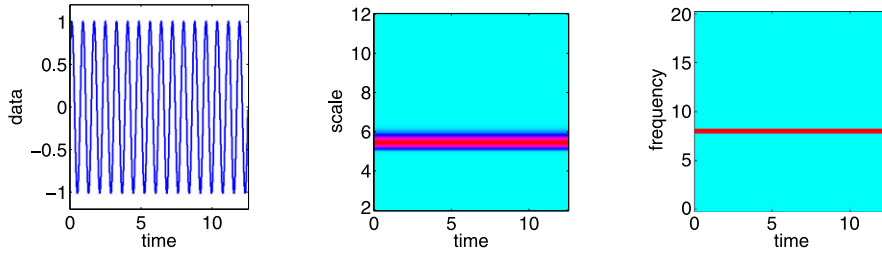


Fig. 5. Left: the harmonic signal $f(t) = \sin(8t)$; middle: the continuous wavelet transform of f ; right: synchrosqueezed transform of f .

2. Synchrosqueezing wavelet transforms

Synchrosqueezing was introduced in the context of analyzing auditory signals [13]; it is a special case of *reallocation methods* [14–16], which aim to “sharpen” a time-frequency representation $\mathcal{R}(t, \omega)$ by “allocating” its value to a different point (t', ω') in the time-frequency plane, determined by the local behavior of $\mathcal{R}(t, \omega)$ around (t, ω) . In the case of synchrosqueezing as defined in [13], one starts from the continuous wavelet transform W_s of the signal s defined by²

$$W_s(a, b) = \int s(t) a^{-1/2} \overline{\psi\left(\frac{t-b}{a}\right)} dt, \quad (2.1)$$

where ψ is an appropriately chosen wavelet, and reallocates the $W_s(a, b)$ to get a concentrated time-frequency picture, from which instantaneous frequency lines can be extracted. An introduction to wavelets and the continuous wavelet transform can be found in many places, e.g. in [17].

To motivate the idea, let us start with a purely harmonic signal,

$$s(t) = A \cos(\omega t).$$

Take a wavelet ψ that is concentrated on the positive frequency axis: $\hat{\psi}(\xi) = 0$ for $\xi < 0$. By Plancherel's theorem, we can rewrite $W_s(a, b)$, the continuous wavelet transform of s with respect to ψ , as

$$\begin{aligned} W_s(a, b) &= \frac{1}{2\pi} \int \hat{s}(\xi) a^{1/2} \overline{\hat{\psi}(a\xi)} e^{ib\xi} d\xi \\ &= \frac{A}{4\pi} \int [\delta(\xi - \omega) + \delta(\xi + \omega)] a^{1/2} \overline{\hat{\psi}(a\xi)} e^{ib\xi} d\xi \\ &= \frac{A}{4\pi} a^{1/2} \overline{\hat{\psi}(a\omega)} e^{ib\omega}. \end{aligned} \quad (2.2)$$

If $\hat{\psi}(\xi)$ is concentrated around $\xi = \omega_0$, then $W_s(a, b)$ will be concentrated around $a = \omega_0/\omega$. However, the wavelet transform $W_s(a, b)$ will be spread out over a region around the horizontal line $a = \omega_0/\omega$ on the time-scale plane. The observation made in [13] is that although $W_s(a, b)$ is spread out in a , its oscillatory behavior in b points to the original frequency ω , regardless of the value of a .

This led to the suggestion to compute, for any (a, b) for which $W_s(a, b) \neq 0$, a candidate instantaneous frequency $\omega_s(a, b)$ for the signal s by

$$\omega_s(a, b) = -i(W_s(a, b))^{-1} \frac{\partial}{\partial b} W_s(a, b). \quad (2.3)$$

For the purely harmonic signal $s(t) = A \cos(\omega t)$, one obtains $\omega_s(a, b) = \omega$, as desired; this is illustrated in Fig. 5. For simplicity, when we expect no confusion to occur, we will suppress the dependence on s and denote $\omega(a, b) = \omega_s(a, b)$. In a next step, the information from the time-scale plane is transferred to the time-frequency plane, according to the map $(b, a) \rightarrow (b, \omega_s(a, b))$, in an operation dubbed *synchrosqueezing*. In [13], the frequency variable ω and the scale variable a were “binned”, i.e. $W_s(a, b)$ was computed only at discrete values a_k , with $a_k - a_{k-1} = (\Delta a)_k$, and its synchrosqueezed transform $T_s(\omega, b)$ was likewise determined only at the centers ω_ℓ of the successive bins $[\omega_\ell - \frac{1}{2}\Delta\omega, \omega_\ell + \frac{1}{2}\Delta\omega]$, with $\omega_\ell - \omega_{\ell-1} = \Delta\omega$, by summing different contributions:

$$T_s(\omega_\ell, b) = (\Delta\omega)^{-1} \sum_{a_k: |\omega(a_k, b) - \omega_\ell| \leq \Delta\omega/2} W_s(a_k, b) a_k^{-3/2} (\Delta a)_k. \quad (2.4)$$

² In this section, as the purpose is to introduce the method, we shall not dwell on the assumptions on the function s and the wavelet ψ so that the expressions and manipulations are justified. In other words, we shall assume that s and ψ are sufficiently nice functions. More careful definitions and justifications will be discussed in the next section when we discuss the mathematical properties of the method.

The following argument shows that the signal can still be reconstructed after the synchrosqueezing. We have

$$\begin{aligned} \int_0^\infty W_s(a, b) a^{-3/2} da &= \frac{1}{2\pi} \int_{-\infty}^\infty \int_0^\infty \hat{s}(\xi) \overline{\hat{\psi}(a\xi)} e^{ib\xi} a^{-1} da d\xi \\ &= \frac{1}{2\pi} \int_0^\infty \int_0^\infty \hat{s}(\xi) \overline{\hat{\psi}(a\xi)} e^{ib\xi} a^{-1} da d\xi \\ &= \int_0^\infty \overline{\hat{\psi}(\xi)} \frac{d\xi}{\xi} \cdot \frac{1}{2\pi} \int_0^\infty \hat{s}(\zeta) e^{ib\zeta} d\zeta. \end{aligned} \quad (2.5)$$

Setting $C_\psi = \frac{1}{2} \int_0^\infty \overline{\hat{\psi}(\xi)} \frac{d\xi}{\xi}$, we then obtain (assuming that s is real, so that $\hat{s}(\xi) = \overline{\hat{s}(-\xi)}$, hence $s(b) = \pi^{-1} \Re \left[\int_0^\infty \hat{s}(\xi) \times e^{ib\xi} d\xi \right]$)

$$s(b) = \Re \left[C_\psi^{-1} \int_0^\infty W_s(a, b) a^{-3/2} da \right]. \quad (2.6)$$

In the piecewise constant approximation corresponding to the binning in a , this becomes

$$s(b) \approx \Re \left[C_\psi^{-1} \sum_k W_s(a_k, b) a_k^{-3/2} (\Delta a)_k \right] = \Re \left[C_\psi^{-1} \sum_\ell T_s(\omega_\ell, b) (\Delta \omega) \right]. \quad (2.7)$$

Remark. As defined above, (2.4) assumes a linear scale discretization of ω . If instead another discretization (e.g., logarithmic discretization) is used, the $\Delta \omega$ has to be made dependent on ℓ ; alternatively, one can also change the exponent of a from $-3/2$ to $-1/2$.

If one chooses (as we shall do here) to continue to treat a and ω as continuous variables, without discretization, the analog of (2.4) is³

$$\mathcal{I}_s(\omega, b) = \int_{A(b)} W_s(a, b) a^{-3/2} \delta(\omega(a, b) - \omega) da, \quad (2.8)$$

where $A(b) = \{a; W_s(a, b) \neq 0\}$, and $\omega(a, b)$ is as defined in (2.3) above, for (a, b) such that $a \in A(b)$.

Remark. In practice, the determination of those (a, b) -pairs for which $W_s(a, b) = 0$ is rather unstable, when s has been contaminated by noise. For this reason, it is often useful to consider a threshold for $|W_s(a, b)|$, below which $\omega(a, b)$ is not defined; this amounts to replacing $A(b)$ by the smaller region $A_\epsilon(b) := \{a; |W_s(a, b)| \geq \epsilon\}$.

3. Main result

We define a class of functions, containing *intrinsic mode type* components that are *well separated*, and show that they can be identified and characterized by means of synchrosqueezing.

We start with the following definitions:

Definition 3.1 (*Intrinsic mode type function*). A continuous function $f : \mathbb{R} \rightarrow \mathbb{C}$, $f \in L^\infty(\mathbb{R})$ is said to be *intrinsic-mode-type* (IMT) with accuracy $\epsilon > 0$ if $f(t) = A(t)e^{i\phi(t)}$ with A and ϕ having the following properties:

$$\begin{aligned} A &\in C^1(\mathbb{R}) \cap L_\infty(\mathbb{R}), \quad \phi \in C^2(\mathbb{R}), \\ \inf_{t \in \mathbb{R}} \phi'(t) &> 0, \quad \sup_{t \in \mathbb{R}} \phi'(t) < \infty, \\ |A'(t)|, |\phi''(t)| &\leq \epsilon |\phi'(t)|, \quad \forall t \in \mathbb{R}, \\ M'' &:= \sup_{t \in \mathbb{R}} |\phi''(t)| < \infty. \end{aligned}$$

³ The expression $\delta(\omega(a, b) - \omega)$ should be interpreted in the sense of distributions; we will come back to this in the next section.

Definition 3.2 (*Superposition of well-separated intrinsic mode components*). A function $f : \mathbb{R} \rightarrow \mathbb{C}$ is said to be a superposition of, or to consist of, *well-separated intrinsic mode components, up to accuracy ϵ , and with separation d* , if there exists a finite K , such that

$$f(t) = \sum_{k=1}^K f_k(t) = \sum_{k=1}^K A_k(t) e^{i\phi_k(t)},$$

where all the f_k are IMT, and where moreover their respective phase functions ϕ_k satisfy

$$\phi'_k(t) > \phi'_{k-1}(t) \quad \text{and} \quad |\phi'_k(t) - \phi'_{k-1}(t)| \geq d[\phi'_k(t) + \phi'_{k-1}(t)], \quad \forall t \in \mathbb{R}.$$

Remark. It is not really necessary for the components f_k to be defined on all of \mathbb{R} . One can also suppose that they are supported on intervals, $\text{supp}(f_k) = \text{supp}(A_k) \subset [-T_k, T_k]$, where the different T_k need not be identical. In this case the various inequalities governing the definition of an IMT function or a superposition of well-separated IMT components must simply be restricted to the relevant intervals. For the inequality above on the $\phi'_k(t)$, $\phi'_{k-1}(t)$, it may happen that some t are covered by (say) $[-T_k, T_k]$ but not by $[-T_{k-1}, T_{k-1}]$; one should then replace $k-1$ by the largest $\ell < k$ for which $t \in [-T_\ell, T_\ell]$; other, similar, changes would have to be made if $t \in [-T_{k-1}, T_{k-1}] \setminus [-T_k, T_k]$.

We omit this extra wrinkle for the sake of keeping notations manageable.

Notation (*Class $\mathcal{A}_{\epsilon,d}$*). We denote by $\mathcal{A}_{\epsilon,d}$ the set of all superpositions of well-separated IMT, up to accuracy ϵ and with separation d .

Remark. The function class $\mathcal{A}_{\epsilon,d}$ defined above is a subset of $L^\infty(\mathbb{R})$. Note that it is just a set of functions but not a vector space: the sum of two elements in $\mathcal{A}_{\epsilon,d}$ is still a superposition of IMT components but they could fail to have separation d , in the sense of the definition above.

Our main result is then the following:

Theorem 3.3. Let f be a function in $\mathcal{A}_{\epsilon,d}$, and set $\tilde{\epsilon} := \epsilon^{1/3}$. Pick a function $h \in C_c^\infty$ with $\int h(t) dt = 1$, and pick a wavelet ψ in Schwartz class such that its Fourier transform $\hat{\psi}$ is supported in $[1 - \Delta, 1 + \Delta]$, with $\Delta < d/(1 + d)$; set $\mathcal{R}_\psi = \sqrt{2\pi} \int \hat{\psi}(\zeta) \zeta^{-1} d\zeta$. Consider the continuous wavelet transform $W_f(a, b)$ of f with respect to this wavelet, as well as the function $S_{f,\tilde{\epsilon}}^\delta(b, \omega)$ obtained by synchrosqueezing W_f , with threshold $\tilde{\epsilon}$ and accuracy δ , i.e.

$$S_{f,\tilde{\epsilon}}^\delta(b, \omega) := \int_{A_{\tilde{\epsilon},f}(b)} W_f(a, b) \frac{1}{\delta} h\left(\frac{\omega - \omega_f(a, b)}{\delta}\right) a^{-3/2} da, \quad (3.1)$$

where $A_{\tilde{\epsilon},f}(b) := \{a \in \mathbb{R}_+; |W_f(a, b)| > \tilde{\epsilon}\}$. Then, provided ϵ (and thus also $\tilde{\epsilon}$) is sufficiently small, the following hold:

- $|W_f(a, b)| > \tilde{\epsilon}$ only when, for some $k \in \{1, \dots, K\}$, $(a, b) \in Z_k := \{(a, b); |a\phi'_k(b) - 1| < \Delta\}$.
- For each $k \in \{1, \dots, K\}$, and for each pair $(a, b) \in Z_k$ for which holds $|W_f(a, b)| > \tilde{\epsilon}$, we have

$$|\omega_f(a, b) - \phi'_k(b)| \leq \tilde{\epsilon}.$$

- Moreover, for each $k \in \{1, \dots, K\}$, there exists a constant C such that, for any $b \in \mathbb{R}$,

$$\left| \lim_{\delta \rightarrow 0} \left(\mathcal{R}_\psi^{-1} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} S_{f,\tilde{\epsilon}}^\delta(b, \omega) d\omega \right) - A_k(b) e^{i\phi_k(b)} \right| \leq C\tilde{\epsilon}.$$

The function $S_{f,\tilde{\epsilon}}^\delta$, defined by (3.1), can be viewed as the “action” of the distribution in (2.8) on the Schwartz function $\delta^{-1}h(\cdot/\delta)$; in the limit for $\delta \rightarrow 0$, $S_{f,\tilde{\epsilon}}^\delta$ tends, in the sense of distributions, to (2.8). Theorem 3.3 basically tells us that, for $f \in \mathcal{A}_{\epsilon,d}$, the (smoothed) synchrosqueezed version $S_{f,\tilde{\epsilon}}^\delta$ of the wavelet transform W_f is concentrated, in the (b, ω) -plane, in narrow bands around the curves $\omega = \phi'_k(b)$, and that the restriction of $S_{f,\tilde{\epsilon}}^\delta$ to the k -th narrow band suffices to reconstruct, with high precision, the k -th IMT component of f . Synchrosqueezing (an appropriate) wavelet transform thus provides the *adaptive time-frequency decomposition* that is the goal of empirical mode decomposition.

The proof of Theorem 3.3 relies on a number of estimates, which we demonstrate one by one, at the same time providing more details about what it means for ϵ to be “sufficiently small”. In the statement and proof of all the estimates in this section, we shall always assume that all the conditions of Theorem 3.3 are satisfied (without repeating them), unless stated otherwise.

The first estimate bounds the growth of the A_k , ϕ'_k in the neighborhood of t , in terms of the value of $|\phi'_k(t)|$.

Estimate 3.4. For each $k \in \{1, \dots, K\}$, we have

$$\begin{aligned} |A_k(t+s) - A_k(t)| &\leq \epsilon |s| \left(|\phi'_k(t)| + \frac{1}{2} M''_k |s| \right) \quad \text{and} \\ |\phi'_k(t+s) - \phi'_k(t)| &\leq \epsilon |s| \left(|\phi'_k(t)| + \frac{1}{2} M''_k |s| \right). \end{aligned}$$

Proof. When $s \geq 0$, we have (the case $s < 0$ can be done in an analogue way)

$$\begin{aligned} |A_k(t+s) - A_k(t)| &= \left| \int_0^s A'_k(t+u) du \right| \\ &\leq \int_0^s |A'_k(t+u)| du \leq \epsilon \int_0^s |\phi'_k(t+u)| du \\ &= \epsilon \int_0^s \left| \phi'_k(t) + \int_0^u \phi''_k(t+x) dx \right| du \\ &\leq \epsilon \left(|\phi'_k(t)| |s| + \frac{1}{2} M''_k |s|^2 \right). \end{aligned}$$

The other bound is analogous. \square

The next estimate shows that, for f and ψ satisfying the conditions in the statement of Theorem 3.3, the wavelet transform $W_f(a, b)$ is concentrated near the regions where, for some $k \in \{1, 2, \dots, K\}$, $a\phi'_k(b)$ is close to 1. (This estimate is similar to the argument in stationary phase approximations, for example, used in [18].)

Estimate 3.5.

$$\left| W_f(a, b) - \sqrt{2\pi} \sum_{k=1}^K A_k(b) e^{i\phi_k(b)} \sqrt{a} \hat{\psi}(a\phi'_k(b)) \right| \leq \epsilon a^{3/2} \Gamma_1(a, b),$$

where

$$\Gamma_1(a, b) := I_1 \sum_{k=1}^K |\phi'_k(b)| + \frac{1}{2} I_2 a \sum_{k=1}^K [M''_k + |A_k(b)| |\phi'_k(b)|] + \frac{1}{6} I_3 a^2 \sum_{k=1}^K M''_k |A_k(b)|,$$

with $I_n := \int |u|^n |\psi(u)| du$.

Proof. Since $f \in \mathcal{A}_{\epsilon, \delta} \subset L^\infty(\mathbb{R})$ and $\psi \in \mathcal{S}$, the continuous wavelet transform of f with respect to ψ is well defined, and we have

$$\begin{aligned} W_f(a, b) &= \sum_{k=1}^K \int A_k(t) e^{i\phi_k(t)} a^{-1/2} \psi\left(\frac{t-b}{a}\right) dt \\ &= \sum_{k=1}^K A_k(b) \int e^{i[\phi_k(b) + \phi'_k(b)(t-b) + \int_0^{t-b} [\phi'_k(b+u) - \phi'_k(b)] du]} a^{-1/2} \psi\left(\frac{t-b}{a}\right) dt \\ &\quad + \sum_{k=1}^K \int [A_k(t) - A_k(b)] e^{i\phi_k(t)} a^{-1/2} \psi\left(\frac{t-b}{a}\right) dt. \end{aligned}$$

Using that

$$\sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \sqrt{a} \hat{\psi}(a\phi'_k(b)) = e^{i(\phi_k(b) - b\phi'_k(b))} \int A_k(b) e^{it\phi'_k(b)} \frac{1}{\sqrt{a}} \psi\left(\frac{t-b}{a}\right) dt,$$

we obtain

$$\begin{aligned}
& \left| W_f(a, b) - \sqrt{2\pi} \sum_{k=1}^K A_k(b) e^{i\phi_k(b)} \sqrt{a} \hat{\psi}\left(a\phi'_k(b)\right) \right| \\
& \leq \sum_{k=1}^K \int |A_k(t) - A_k(b)| a^{-1/2} \left| \psi\left(\frac{t-b}{a}\right) \right| dt \\
& \quad + \sum_{k=1}^K |A_k(b)| \int |e^{i \int_0^{t-b} [\phi'_k(b+u) - \phi'_k(b)] du} - 1| a^{-1/2} \left| \psi\left(\frac{t-b}{a}\right) \right| dt \\
& \leq \sum_{k=1}^K \int \epsilon |t-b| \left(|\phi'_k(b)| + \frac{1}{2} M''_k |t-b| \right) a^{-1/2} \left| \psi\left(\frac{t-b}{a}\right) \right| dt \\
& \quad + \sum_{k=1}^K |A_k(b)| \int \left| \int_0^{t-b} [\phi'_k(b+u) - \phi'_k(b)] du \right| a^{-1/2} \left| \psi\left(\frac{t-b}{a}\right) \right| dt \\
& \leq \epsilon \sum_{k=1}^K \left[a^{3/2} |\phi'_k(b)| \int |u| |\psi(u)| du + a^{5/2} \frac{1}{2} M''_k \int |u|^2 |\psi(u)| du \right] \\
& \quad + \sum_{k=1}^K |A_k(b)| \epsilon \int \left[\frac{1}{2} |t-b|^2 |\phi'_k(b)| + \frac{1}{6} |t-b|^3 M''_k \right] a^{-1/2} \left| \psi\left(\frac{t-b}{a}\right) \right| dt \\
& \leq \epsilon a^{3/2} \left\{ I_1 \sum_{k=1}^K |\phi'_k(b)| + \frac{1}{2} I_2 a \sum_{k=1}^K [M''_k + |A_k(b)| |\phi'_k(b)|] + \frac{1}{6} I_3 a^2 \sum_{k=1}^K M''_k |A_k(b)| \right\}. \quad \square \tag{3.2}
\end{aligned}$$

The wavelet ψ satisfies $\hat{\psi}(\xi) \neq 0$ only for $1 - \Delta < \xi < 1 + \Delta$; it follows that $|W_f(a, b)| \leq \epsilon a^{3/2} \Gamma_1(a, b)$ whenever $|a\phi'_k(b) - 1| > \Delta$ for all $k \in \{1, \dots, K\}$. On the other hand, we also have the following lemma:

Lemma 3.6. *For any pair (a, b) under consideration, there can be at most one $k \in \{1, \dots, K\}$ for which $|a\phi'_k(b) - 1| < \Delta$.*

Proof. Suppose that $k, \ell \in \{1, \dots, K\}$ both satisfy the condition, i.e. that $|a\phi'_k(b) - 1| < \Delta$ and $|a\phi'_\ell(b) - 1| < \Delta$, with $k \neq \ell$. For the sake of definiteness, assume $k > \ell$. Since $f \in \mathcal{A}_{\epsilon, d}$, we have

$$\phi'_k(b) - \phi'_\ell(b) \geq \phi'_k(b) - \phi'_{k-1}(b) \geq d[\phi'_k(b) + \phi'_{k-1}(b)] \geq d[\phi'_k(b) + \phi'_\ell(b)].$$

Combined with

$$\begin{aligned}
\phi'_k(b) - \phi'_\ell(b) & \leq a^{-1} [(1 + \Delta) - (1 - \Delta)] = 2a^{-1} \Delta, \\
\phi'_k(b) + \phi'_\ell(b) & \geq a^{-1} [(1 - \Delta) + (1 - \Delta)] = 2a^{-1} (1 - \Delta),
\end{aligned}$$

this gives

$$\Delta \geq d(1 - \Delta),$$

which contradicts the condition $\Delta < d/(1 + d)$ from Theorem 3.3. \square

It follows that the (a, b) -plane contains K non-touching “zones” given as $Z_k = \{|a\phi'_k(b) - 1| < \Delta\}$, $k \in \{1, \dots, K\}$, separated by a “no-man’s land” where $|W_f(a, b)|$ is small. Note that the lower and upper bounds on $\phi'_k(b)$ imply that the values of a for which $(a, b) \in Z_k$, for some $k \in \{1, \dots, K\}$, are uniformly bounded from above and from below. It then follows that $\Gamma_1(a, b)$ is uniformly bounded as well, for $(a, b) \in \bigcup_{k=1}^K Z_k$, and that $\inf\{a^{-9/4} \Gamma_1^{-3/2}(a, b); (a, b) \in \bigcup_{k=1}^K Z_k\} > 0$. We shall assume (see below) that ϵ is sufficiently small, i.e., that for all $(a, b) \in \bigcup_{k=1}^K Z_k$,

$$\epsilon < a^{-9/4} \Gamma_1^{-3/2}(a, b), \tag{3.3}$$

so that $\epsilon a^{3/2} \Gamma_1(a, b) < \epsilon^{1/3} = \tilde{\epsilon}$. The upper bound in the intermediate region between the zones Z_k is then below the threshold $\tilde{\epsilon}$ allowed for the computation of $\omega_f(a, b)$ used in $S_{f, \tilde{\epsilon}}$ (see the formulation of Theorem 3.3). It follows that we will compute $\omega_f(a, b)$ only in the special zones themselves. We thus need to estimate $\partial_b W_f(a, b)$ in each of these zones.

Estimate 3.7. For $k \in \{1, \dots, K\}$, and $(a, b) \in \mathbb{R}_+ \times \mathbb{R}$ such that $|a\phi'_k(b) - 1| < \Delta$, we have

$$|-i\partial_b W_f(a, b) - \sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \sqrt{a} \phi'_k(b) \hat{\psi}(a\phi'_k(b))| \leq \epsilon a^{1/2} \Gamma_2(a, b),$$

where

$$\Gamma_2(a, b) := I'_1 \sum_{\ell=1}^K |\phi'_\ell(b)| + \frac{1}{2} I'_2 a \sum_{\ell=1}^K [M''_\ell + |A_\ell(b)| |\phi'_\ell(b)|] + \frac{1}{6} I'_3 a^2 \sum_{\ell=1}^K M''_\ell |A_\ell(b)|,$$

with $I'_n := \int |u|^n |\psi'(u)| du$.

(Note that, like Γ_1 , $\Gamma_2(a, b)$ is uniformly bounded for $(a, b) \in \bigcup_{k=1}^K Z_k$, by essentially the same argument.)

Proof. The proof follows the same lines as that for Estimate 3.5. Since $\psi \in \mathcal{S}$, we obtain (by using the Dominant Convergence theorem) that

$$\begin{aligned} \partial_b W_f(a, b) &= \partial_b \left(\sum_{\ell=1}^K \int A_\ell(t) e^{i\phi_\ell(t)} a^{-1/2} \psi\left(\frac{t-b}{a}\right) dt \right) \\ &= - \sum_{\ell=1}^K \int A_\ell(t) e^{i\phi_\ell(t)} a^{-3/2} \psi'\left(\frac{t-b}{a}\right) dt \\ &= - \sum_{\ell=1}^K A_\ell(b) \int e^{i[\phi_\ell(b) + \phi'_\ell(b)(t-b) + \int_0^{t-b} [\phi'_\ell(b+u) - \phi'_\ell(b)] du]} a^{-3/2} \psi'\left(\frac{t-b}{a}\right) dt \\ &\quad - \sum_{\ell=1}^K \int [A_\ell(t) - A_\ell(b)] e^{i\phi_\ell(t)} a^{-3/2} \psi'\left(\frac{t-b}{a}\right) dt. \end{aligned} \quad (3.4)$$

By Lemma 3.6, only the term for $\ell = k$ is nonzero in the sum for (a, b) such that $|a\phi'_k(b) - 1| < \Delta$. Also note that

$$\begin{aligned} &\sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \sqrt{a} \phi'_k(b) \hat{\psi}(a\phi'_k(b)) \\ &= e^{i(\phi_k(b) - b\phi'_k(b))} \int A_k(b) e^{it\phi'_k(b)} \frac{1}{\sqrt{a}} \psi\left(\frac{t-b}{a}\right) \phi'_k(b) dt \\ &= i e^{i(\phi_k(b) - b\phi'_k(b))} \int A_k(b) e^{it\phi'_k(b)} \frac{1}{a^{3/2}} \psi'\left(\frac{t-b}{a}\right) dt. \end{aligned}$$

Thus for (a, b) such that $|a\phi'_k(b) - 1| < \Delta$,

$$\begin{aligned} \partial_b W_f(a, b) &= -A_k(b) \int e^{i[\phi_k(b) + \phi'_k(b)(t-b) + \int_0^{t-b} [\phi'_k(b+u) - \phi'_k(b)] du]} a^{-3/2} \psi'\left(\frac{t-b}{a}\right) dt \\ &\quad - \int [A_k(t) - A_k(b)] e^{i\phi_k(t)} a^{-3/2} \psi'\left(\frac{t-b}{a}\right) dt, \end{aligned}$$

and we obtain

$$\begin{aligned} &|\partial_b W_f(a, b) - i\sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \sqrt{a} \phi'_k(b) \hat{\psi}(a\phi'_k(b))| \\ &= \left| \partial_b W_f(a, b) - \sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \frac{1}{\sqrt{a}} \hat{\psi}'(a\phi'_k(b)) \right| \\ &\leq \sum_{\ell=1}^K \int \epsilon |t-b| \left(|\phi'_\ell(b)| + \frac{1}{2} M''_\ell |t-b| \right) a^{-3/2} \left| \psi'\left(\frac{t-b}{a}\right) \right| dt \\ &\quad + \sum_{\ell=1}^K |A_k(b)| \int \left| e^{i \int_0^{t-b} [\phi'_\ell(b+u) - \phi'_\ell(b)] du} - 1 \right| a^{-3/2} \left| \psi'\left(\frac{t-b}{a}\right) \right| dt \\ &\leq \epsilon \sum_{\ell=1}^K \left[a^{1/2} |\phi'_\ell(b)| \int |u| |\psi'(u)| du + a^{3/2} \frac{1}{2} M''_\ell \int |u|^2 |\psi'(u)| du \right] \end{aligned}$$

$$\begin{aligned}
& + \epsilon \sum_{\ell=1}^K |A_\ell(b)| \int \left[\frac{1}{2} |t-b|^2 |\phi'_\ell(b)| + \frac{1}{6} |t-b|^3 M''_\ell \right] a^{-3/2} \left| \psi' \left(\frac{t-b}{a} \right) \right| dt \\
& \leq \epsilon a^{1/2} \sum_{\ell=1}^K \left\{ I'_1 |\phi'_\ell(b)| + \frac{1}{2} I'_2 a [M''_\ell + |A_\ell(b)| |\phi'_\ell(b)|] + \frac{1}{6} I'_3 a^2 M''_\ell |A_\ell(b)| \right\}. \quad \square
\end{aligned}$$

Combining Estimates 3.5 and 3.7, we find

Estimate 3.8. Suppose that (3.3) is satisfied. For $k \in \{1, \dots, K\}$, and $(a, b) \in \mathbb{R}_+ \times \mathbb{R}$ such that both $|a\phi'_k(b) - 1| < \Delta$ and $W_f(a, b) \geq \tilde{\epsilon}$ are satisfied, we have

$$|\omega_f(a, b) - \phi'_k(b)| \leq \sqrt{a}(\Gamma_2 + a\Gamma_1\phi'_k(b))\epsilon^{2/3}.$$

Proof. By definition,

$$\omega_f(a, b) = \frac{-i\partial_b W_f(a, b)}{W_f(a, b)}.$$

For convenience, let us, for this proof only, use the short-hand notation $B = \sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \sqrt{a} \hat{\psi}(a\phi'_k(b))$. For the (a, b) -pairs under consideration, we have then

$$|-i\partial_b W_f(a, b) - \phi'_k(b)B| \leq \epsilon a^{1/2} \Gamma_2 \quad \text{and} \quad |W_f(a, b) - B| \leq \epsilon a^{3/2} \Gamma_1.$$

Using $\tilde{\epsilon} = \epsilon^{1/3}$, it follows that

$$\omega_f(a, b) - \phi'_k(b) = \frac{-i\partial_b W_f(a, b) - \phi'_k(b)B}{W_f(a, b)} + \frac{[B - W_f(a, b)]\phi'_k(b)}{W_f(a, b)},$$

so that

$$\begin{aligned}
|\omega_f(a, b) - \phi'_k(b)| & \leq \frac{\epsilon a^{1/2} \Gamma_2 + \epsilon a^{3/2} \phi'_k(b) \Gamma_1}{W_f(a, b)} \\
& \leq \sqrt{a}(\Gamma_2 + a\Gamma_1\phi'_k(b))\epsilon^{2/3}. \quad \square
\end{aligned}$$

If (see below) we impose an extra restriction on ϵ , namely that, for all $k \in \{1, 2, \dots, K\}$ and all $(a, b) \in \{(a, b); |a\phi'_k(b) - 1| < \Delta, W_f(a, b) \geq \tilde{\epsilon}\} \subset Z_k$,

$$0 < \epsilon < a^{-3/2} [\Gamma_2(a, b) + a\phi'_k(b)\Gamma_1(a, b)]^{-3} \quad (3.5)$$

(note that the right-hand side is uniformly bounded below, away from zero, for $(a, b) \in \bigcup_{k=1}^K Z_k$, guaranteeing the existence of $\epsilon > 0$ that can satisfy this inequality), then this last estimate can be simplified to

$$|\omega_f(a, b) - \phi'_k(b)| < \tilde{\epsilon}. \quad (3.6)$$

Next is our final estimate:

Estimate 3.9. Suppose that both (3.3) and (3.5) are satisfied, and that, in addition, for all b under consideration,

$$\epsilon \leq 1/8d^3 [\phi'_1(b) + \phi'_2(b)]^3. \quad (3.7)$$

Let $S_{f, \tilde{\epsilon}}^\delta$ be the synchrosqueezed wavelet transform of f with accuracy δ ,

$$S_{f, \tilde{\epsilon}}^\delta(b, \omega) := \int_{A_{\tilde{\epsilon}, f}(b)} W_f(a, b) \frac{1}{\delta} h\left(\frac{\omega - \omega_f(a, b)}{\delta}\right) a^{-3/2} da.$$

Then we have, for all $b \in \mathbb{R}$, and all $k \in \{1, \dots, K\}$

$$\left| \lim_{\delta \rightarrow 0} \mathcal{R}_\psi^{-1} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} S_{f, \tilde{\epsilon}}(b, \omega) d\omega - A_k(b) e^{i\phi_k(b)} \right| \leq C\tilde{\epsilon}.$$

Proof. For later use, note first that (3.7) implies that, for all $k, \ell \in \{1, \dots, K\}$,

$$d[\phi'_k(b) + \phi'_\ell(b)] > 2\tilde{\epsilon}. \quad (3.8)$$

For a fixed $b \in \mathbb{R}$ under consideration, since $W_f(a, b) \in C^\infty(A_{\tilde{\epsilon}, f}(b))$, where $A_{\tilde{\epsilon}, f}(b)$ is inside the compact set $\bigcup_{k=1}^K Z_k$ away from zero, clearly $S_{f, \tilde{\epsilon}}^\delta(b, \omega) \in C^\infty(\mathbb{R})$. We have

$$\begin{aligned} \lim_{\delta \rightarrow 0} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} S_{f, \tilde{\epsilon}}^\delta(b, \omega) d\omega &= \lim_{\delta \rightarrow 0} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} \int_{A_{\tilde{\epsilon}, f}(b)} W_f(a, b) \frac{1}{\delta} h\left(\frac{\omega - \omega_f(a, b)}{\delta}\right) a^{-3/2} da d\omega \\ &= \lim_{\delta \rightarrow 0} \int_{A_{\tilde{\epsilon}, f}(b)} a^{-3/2} W_f(a, b) \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} \frac{1}{\delta} h\left(\frac{\omega - \omega_f(a, b)}{\delta}\right) d\omega da \\ &= \int_{A_{\tilde{\epsilon}, f}(b)} a^{-3/2} W_f(a, b) \lim_{\delta \rightarrow 0} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} \frac{1}{\delta} h\left(\frac{\omega - \omega_f(a, b)}{\delta}\right) d\omega da \\ &= \int_{A_{\tilde{\epsilon}, f}(b) \cap \{a; |\omega_f(a, b) - \phi'_k(b)| < \tilde{\epsilon}\}} W_f(a, b) a^{-3/2} da, \end{aligned}$$

where we have used the Fubini theorem for the second equality, and the Dominant Convergence theorem for the third and fourth equalities: the integrand is bounded by $a^{-3/2} W_f(a, b) \in L^1(A_{\tilde{\epsilon}, f}(b))$ and converges a.e. to $a^{-3/2} W_f(a, b)$ if $|\omega_f(a, b) - \phi'_k(b)| < \tilde{\epsilon}$, and to zero if $|\omega_f(a, b) - \phi'_k(b)| > \tilde{\epsilon}$. From Estimate 3.5 and (3.3) we know that $|W_f(a, b)| > \tilde{\epsilon}$ only when $|a\phi'_\ell(b) - 1| < \Delta$ for some $\ell \in \{1, \dots, K\}$. When $\ell \neq k$, we have, by Estimate 3.8, that $|a\phi'_\ell(b) - 1| < \Delta$ implies (use (3.8))

$$\begin{aligned} |\omega_f(a, b) - \phi'_k(b)| &\geq |\phi'_\ell(b) - \phi'_k(b)| - |\omega_f(a, b) - \phi'_\ell(b)| \\ &\geq d[\phi'_\ell(b) + \phi'_k(b)] - \tilde{\epsilon} > \tilde{\epsilon}. \end{aligned}$$

It follows that there is only one ℓ for which $|a\phi'_\ell(b) - 1| < \Delta$ and $|\omega_f(a, b) - \phi'_k(b)| < \tilde{\epsilon}$ hold simultaneously, namely $\ell = k$. Hence

$$\begin{aligned} \lim_{\delta \rightarrow 0} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} S_{f, \tilde{\epsilon}}^\delta(b, \omega) d\omega &= \int_{A_{\tilde{\epsilon}, f}(b) \cap \{|a\phi'_k(b) - 1| < \Delta\}} W_f(a, b) a^{-3/2} da \\ &= \left(\int_{|a\phi'_k(b) - 1| < \Delta} W_f(a, b) a^{-3/2} da \right) - \left(\int_{\{|a\phi'_k(b) - 1| < \Delta\} \setminus A_{\tilde{\epsilon}, f}(b)} W_f(a, b) a^{-3/2} da \right). \end{aligned}$$

From Estimate 3.5 we then obtain

$$\begin{aligned} &\left| \lim_{\delta \rightarrow 0} \mathcal{R}_\psi^{-1} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} S_{f, \tilde{\epsilon}}^\delta(b, \omega) d\omega - A_k(b) e^{i\phi_k(b)} \right| \\ &\leq \left| \mathcal{R}_\psi^{-1} \left(\int_{|a\phi'_k(b) - 1| < \Delta} W_f(a, b) a^{-3/2} da \right) - A_k(b) e^{i\phi_k(b)} \right| + \left| \mathcal{R}_\psi^{-1} \int_{\{|a\phi'_k(b) - 1| < \Delta\} \setminus A_{\tilde{\epsilon}, f}(b)} W_f(a, b) a^{-3/2} da \right| \\ &\leq \left| \mathcal{R}_\psi^{-1} \sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \left(\int_{|a\phi'_k(b) - 1| < \Delta} \sqrt{a} \hat{\psi}(a\phi'_k(b)) a^{-3/2} da \right) - A_k(b) e^{i\phi_k(b)} \right| \\ &\quad + \mathcal{R}_\psi^{-1} \int_{|a\phi'_k(b) - 1| < \Delta} [\tilde{\epsilon} + \tilde{\epsilon} a^{-3/2}] da. \end{aligned}$$

The first term on the right-hand side vanishes, since

$$\begin{aligned} &\mathcal{R}_\psi^{-1} \sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \int_{|a\phi'_k(b) - 1| < \Delta} \hat{\psi}(a\phi'_k(b)) a^{-1} da \\ &= \mathcal{R}_\psi^{-1} \sqrt{2\pi} A_k(b) e^{i\phi_k(b)} \int_{|\zeta - 1| < \Delta} \hat{\psi}(\zeta) \zeta^{-1} d\zeta = A_k(b) e^{i\phi_k(b)}, \end{aligned}$$

by the definition of \mathcal{R}_ψ . In the second term, the integrals can be worked out explicitly. We thus obtain

$$\left| \lim_{\delta \rightarrow 0} \mathcal{R}_\psi^{-1} \int_{|\omega - \phi'_k(b)| < \tilde{\epsilon}} S_{f,\tilde{\epsilon}}^\delta(t, \omega) d\omega - A_k(b) e^{i\phi_k(b)} \right| \leq 2\tilde{\epsilon} \mathcal{R}_\psi^{-1} \left[\frac{\Delta}{\phi'_k(b)} + \left(\frac{\phi'_k(b)}{1 - \Delta} \right)^{1/2} - \left(\frac{\phi'_k(b)}{1 + \Delta} \right)^{1/2} \right]. \quad \square$$

It is now easy to see that all the estimates together provide a complete proof for Theorem 3.3.

Remark. We have three different conditions on ϵ , namely (3.3), (3.5) and (3.7). The auxiliary quantities in these inequalities depend on a and b , and the conditions should be satisfied for all (a, b) -pairs under consideration. This is not really a problem: we saw that the conditions on $A_k(b)$ and $\phi'_k(b)$ imply that there exists an interval of positive measure in which all elements satisfy the three conditions. Note that the different terms can be traded off in many other ways than what is done here; no effort has been made to optimize the bounds, and they can surely be improved. The focus here was not on optimizing the constants, but on proving that, if the rate of change (in time) of the $A_k(b)$ and the $\phi'_k(b)$ is small, compared with the rate of change of the $\phi_k(b)$ themselves, then synchrosqueezing will identify both the “instantaneous frequencies” and their amplitudes.

In the statement of Theorem 3.3, we required the wavelet ψ to be in Schwartz class and have a compactly supported Fourier transform. These assumptions are not absolutely necessary; it was done here for convenience in the proof. For example, if $\hat{\psi}$ is not compactly supported, then extra terms occur in many of the estimates, taking into account the decay of $\hat{\psi}(\zeta)$ as $\zeta \rightarrow \infty$ or $\zeta \rightarrow 0$; these can be handled in ways similar to what we saw above, at the cost of significantly lengthening the computations without making a conceptual difference.

4. A variational approach

The construction and estimates in this section can also be interpreted in a variational framework.

Let us go back to the notion of “instantaneous frequency”. Consider a signal $s(t)$ that is a sum of IMT components $s_i(t)$:

$$s(t) = \sum_{i=1}^N s_i(t) = \sum_{i=1}^N A_i(t) \cos(\phi_i(t)), \quad (4.1)$$

with the additional constraints that $\phi'_i(t)$ and $\phi'_j(t)$ for $i \neq j$ are “well separated”, so that it is reasonable to consider the s_i as individual components. According to the philosophy of EMD, the instantaneous frequency at time t , for the i -th component, is then given by $\omega_i(t) = \phi'_i(t)$.

How could we use this to build a time-frequency representation for s ? If we restrict ourselves to a small window in time around T , of the type $[T - \Delta t, T + \Delta t]$, with $\Delta t \approx 2\pi/\phi'_i(T)$, then (by its IMT nature) the i -th component can be written (approximately) as

$$s_i(t)|_{[T-\Delta t, T+\Delta t]} \approx A_i(T) \cos[\phi_i(T) + \phi'_i(T)(t - T)],$$

which is essentially a truncated Taylor expansion in which terms on the order $\mathcal{O}(A'_i(T))$, $\mathcal{O}(\phi''_i(T))$ have been neglected. Introducing $\omega_i(T) = \phi'_i(T)$, and the phase $\varphi_i(T) := \phi_i(T) - \omega_i(T)T$ we can rewrite this as

$$s_i(t)|_{[T-\Delta t, T+\Delta t]} \approx A_i(T) \cos[\omega_i(T)t + \varphi_i(T)].$$

This signal has a time-frequency representation, as a bivariate “function” of time and frequency, given by (for $t \in [T - \Delta t, T + \Delta t]$)

$$F_i(t, \omega) = A_i(T) \cos[\omega t + \varphi_i(T)] \delta(\omega - \omega_i(T)), \quad (4.2)$$

where δ is the Dirac-delta measure. The time-frequency representation for the full signal $s = \sum_{i=1}^N s_i$, still in the neighborhood of $t = T$, would then be

$$F(t, \omega) = \sum_{i=1}^N A_i(T) \cos[\omega t + \varphi_i(T)] \delta(\omega - \omega_i(T)). \quad (4.3)$$

Integrating over ω , in the neighborhood of $t = T$, leads to $s(t) \approx \int F(t, \omega) d\omega$.

All this becomes even simpler if we introduce the “complex form” of the time-frequency representation: for t near T , we have

$$\tilde{F}(t, \omega) = \sum_{j=1}^N \tilde{A}_j(T) \exp(i\omega t) \delta(\omega - \phi'_j(T)),$$

with $\tilde{A}_j(T) = A_j(T) \exp[i\varphi_j(T)]$; integration over ω now leads to

$$\Re \left[\int \tilde{F}(t, \omega) d\omega \right] = \Re \left[\sum_{j=1}^N A_j(T) \exp[i\omega_j(T)t + i\varphi_j(T)] \right] \approx s(t). \quad (4.4)$$

Note that, because of the presence of the δ -measure, and under the assumption that the components remain separated, the time-frequency function $F(t, \omega)$ satisfies the equation

$$\partial_t \tilde{F}(t, \omega) = i\omega \tilde{F}(t, \omega). \quad (4.5)$$

To get a representation over a longer time interval, the small pieces described above have to be knitted together. One way of doing this is to set $\tilde{F}(t, \omega) = \sum_{j=1}^N \tilde{A}_j(t) \exp(i\omega t) \delta(\omega - \omega_j(t))$. This more globally defined $\tilde{F}(t, \omega)$ is still supported on the N curves given by $\omega = \omega_j(t)$, corresponding to the instantaneous frequency “profile” of the different components. The complex “amplitudes” $\tilde{A}_j(t)$ are given by $\tilde{A}_j(t) = A_j(t) \exp[i\varphi_j(t)]$, where, to determine the phases $\exp[i\varphi_j(t)]$, it suffices to know them at one time t_0 . We have indeed

$$\frac{d\varphi_j(t)}{dt} = \frac{d}{dt} [\phi_j(t) - \omega_j(t)t] = \phi'_j(t) - \omega_j(t) - \omega'_j(t)t = -\omega'_j(t)t;$$

since the $\omega_j(t)$ are known (they are encoded in the support of \tilde{F}), we can compute the $\varphi_j(t)$ by using

$$\varphi_j(t) = - \int_{t_0}^t \omega'_j(\tau) \tau d\tau + \varphi_j(t_0).$$

Moreover, (4.5) still holds (in the sense of distributions) up to terms of size $\mathcal{O}(A'_i(T))$, $\mathcal{O}(\phi''_i(T))$, since

$$\begin{aligned} \partial_t \tilde{F}(t, \omega) &= \sum_{j=1}^N [A'_j(t) - i\omega'_j(t)t A_j(t) + i\omega A_j(t)] e^{i\omega t} \delta(\omega - \omega_j(t)) + A_j(t) e^{i\omega t} \omega'_j(t) \delta'(\omega - \omega_j(t)) \\ &= i\omega \sum_{j=1}^N A_j(t) e^{i\omega t} \delta(\omega - \omega_j(t)) + \mathcal{O}(A'_i(T), \phi''_i(T)) \\ &= i\omega \tilde{F}(t, \omega) + \mathcal{O}(A'_i(T), \phi''_i(T)). \end{aligned}$$

This suggests modeling the adaptive time-frequency decomposition as a variational problem in which one seeks to minimize

$$\int \left| \Re \left[\int F(t, \omega) d\omega \right] - s(t) \right|^2 dt + \mu \iint |\partial_t F(t, \omega) - i\omega F(t, \omega)|^2 dt d\omega \quad (4.6)$$

to which extra terms could be added, such as, $\gamma \iint |F(t, \omega)|^2 dt d\omega$ (corresponding to the constraint that $F \in L^2(\mathbb{R}^2)$), or $\lambda \int [\int |F(t, \omega)|^2 d\omega]^2 dt$ (corresponding to a sparsity constraint in ω for each value of t). Using estimates similar to those in Section 3, one can prove that if $s \in \mathcal{A}_{\epsilon, d}$, then its synchrosqueezed wavelet transform $S_{s, \tilde{\epsilon}}(b, \omega)$ is close to the minimizer of (4.6). Because the estimates and techniques of proof are essentially the same as in Section 3, we don't give the details of this analysis here.

Note that wavelets or wavelet transforms play no role in the variational functional – this fits with our numerical observation that although the wavelet transform itself of s is definitely influenced by the choice of ψ , the dependence on ψ is (almost) completely removed when one considers the synchrosqueezed wavelet transform, at least for signals in $\mathcal{A}_{\epsilon, d}$.

5. Numerical results

In this section we illustrate the effectiveness of synchrosqueezed wavelet transforms on several examples. For all the examples in this section, synchrosqueezing was carried out starting from a Morlet wavelet transform; other wavelets that are well localized in frequency give similar results. The code of synchrosqueezing is available upon requests to the authors.

5.1. Instantaneous frequency profiles for synthesized data

We start by revisiting the toy signal of Figs. 1 and 2 in the Introduction. Fig. 6 shows the result of synchrosqueezing the wavelet transform of this toy signal. We next explore the tolerance to noise of synchrosqueezed wavelet transforms. We denote by $X(t)$ a white noise with zero mean and variance $\sigma^2 = 1$. The *Signal-to-Noise Ratio (SNR)* (measured in dB), will be defined (as usual) by

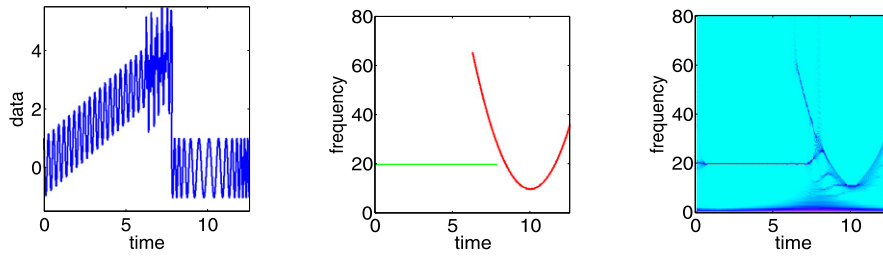


Fig. 6. Revisiting the toy example from the Introduction. Left: the toy signal used for Figs. 1 and 2; middle: its instantaneous frequency; right: the result of synchrosqueezing for this signal. The “extra” component at very low frequency is due to the signal’s not being centered around 0.

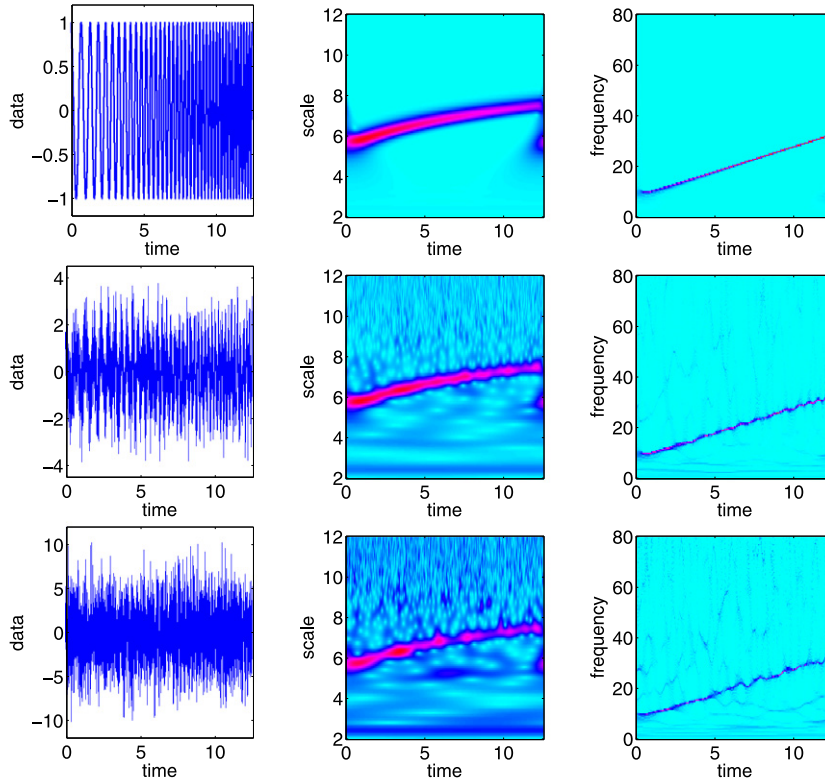


Fig. 7. Top row: left: single chirp signal without noise; middle: its continuous wavelet transform, and right: the synchrosqueezed transform. Middle row: same, after white noise with SNR of -3.00 dB was added to the chirp signal. Lower row: same, now with white noise with SNR of -12.55 dB.

$$\text{SNR [dB]} = 10 \log_{10} \left(\frac{\text{Var } f}{\sigma^2} \right),$$

where f is the noiseless signal. Fig. 7 shows the results of applying our algorithm to a signal consisting of one single chirp function $f(t) = \cos(8t + t^2)$, without noise (i.e. the signal is just f), with some noise (the signal is $f + X$, $\text{SNR} = -3.00$ dB), and with more noise ($f + 3X$, $\text{SNR} = -12.55$ dB). Despite the high noise levels, the synchrosqueezing algorithm identifies the component with reasonable accuracy. Fig. 10 below shows the instantaneous frequency curve extracted from these synchrosqueezed transforms, for the three cases.

Finally we try out a “crossover signal”, that is, a signal composed of two components with instantaneous frequency trajectories that intersect; in our example $f(t) = \cos(t^2 + t + \cos(t)) + \cos(8t)$. Fig. 8 shows the signals $f(t)$ and $f(t) + 0.5X(t)$, together with their synchrosqueezed wavelet transforms, as well as the “ideal” frequency profile given by the instantaneous frequencies of the two components of f .

5.2. Extracting individual components from synthesized data

In many applications listed in [4,5,2,6,7], the desired end goal is the instantaneous frequency trajectory or profile for the different components. When this is the case, the result of the synchrosqueezed wavelet transform, as illustrated in the preceding subsection, provides a solution.

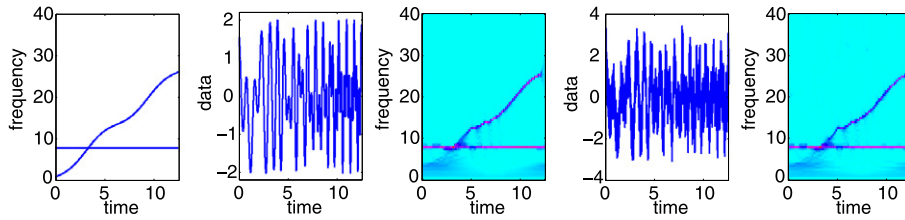


Fig. 8. Far left: the instantaneous frequencies, $\omega(t) = 2t + 1 - \sin(t)$ and 8, of the two IMT components of the crossover signal $f(t) = \cos[t^2 + t + \cos(t)] + \cos(8t)$; middle left: plot of $f(t)$ with no noise added; middle: synchrosqueezed wavelet transforms of noiseless $f(t)$; middle right: $f(t) + \text{noise}$ (corresponding to SNR of 6.45 dB); far right: synchrosqueezed wavelet transforms of $f(t) + \text{noise}$.

In other applications, however, one may wish to consider the individual components themselves. These are obtained as an intermediary result, before extracting instantaneous frequency profiles, in the EMD and EEMD approaches. With synchrosqueezing, they can be obtained in an additional step *after* the frequency profiles have been determined.

Recall that, like most linear time-frequency representations, the wavelet transform comes equipped with reconstruction formulas,

$$f(t) = C_\psi \int_{-\infty}^{\infty} \int_0^{\infty} W_f(a, b) a^{-5/2} \psi\left(\frac{t-b}{a}\right) da db, \quad (5.1)$$

$$\text{as well as } f(t) = C'_\psi \int_0^{\infty} W_f(a, t) a^{-3/2} da = C'_\psi \Re \left[\int_0^{\infty} T_f(t, \omega) d\omega \right], \quad (5.2)$$

where C_ψ, C'_ψ are constants depending only on ψ . For the signals of interest to us here, the synchrosqueezed representation has, as illustrated in the preceding subsection, well-localized zones of concentration. One can use these to select the zone corresponding to one component, and then integrate, in the reconstruction formulas, over the corresponding subregion of the integration domain. In practice, it turns out that the best results are obtained by using the reconstruction formula (5.1).

We illustrate this with the crossover example from the previous subsection: Fig. 9 shows examples of zones selected in the synchrosqueezed transform plane as well as the corresponding reconstructed components. The zones selected in this example have a fixed width and are centered around the concentrated time-frequency curve on the synchrosqueezed wavelet representation. The synchrosqueezed representation is very concentrated, so that the choice of the width of the zone is not crucial: the results remain the same for a wide range of choices for this width. This figure also shows the components obtained for these signals by EMD for the clean case, and by EEMD (more robust to noise than EMD) for the noisy case; for this type of signal, the synchrosqueezed transform proposed here seems to give a more easily interpretable result.

Once the individual components are extracted, one can use them to get a numerical estimate for the variation in time of the instantaneous frequencies of the different components. To illustrate this, we revisit the chirp signal from the previous subsection. Fig. 10 shows the frequency curves obtained by the synchrosqueezing approach; they are fairly robust with respect to noise.

5.3. Applying the synchrosqueezed transform to some real data

So far, all the examples shown concerned toy models or synthesized data. In the subsection we illustrate the result on some real data sets, of medical origin.

5.3.1. Surface electromyography data

In this application, we detrend surface electromyography (sEMG) [19] data acquired from a healthy young female with a portable system (QuickAmp), and exhibit the different IMT components making up the sEMG signal. The sEMG electrodes, with sensors of high-purity sintered Ag/AgCl, were placed on the triceps. The signal was measured for 608 seconds, sampled at 500 Hz. During the data acquisition, the subject flexed/extended her elbow, according to a protocol in which instructions to flex the right or left elbow were given to the subject at not completely regular time intervals; the subject did not know prior to each instruction which elbow she would be told to flex, and the sequence of left/right choices was random. The raw sEMG data $s_l(t)$ and $s_r(t)$ are shown in the left column in Fig. 11.

The middle column in Fig. 11 shows the results $\mathcal{W}_{s_l}(t, \omega)$, $\mathcal{W}_{s_r}(t, \omega)$ of our synchrosqueezing algorithm applied to the two sEMG data sets. We used an implementation in which each dyadic scale interval ($a \in [2^k, 2^{k+1}]$) was divided into 32 equi-log-spaced bins.

The original surface electromyography signals show an erratic drift, which medical researchers wish to remove without losing any sharpness in the peaks. To achieve this, we identified the low frequency components (i.e. the dominant components at frequencies below 1 Hz) in the signal, and removed them before reconstruction. More, precisely, we defined

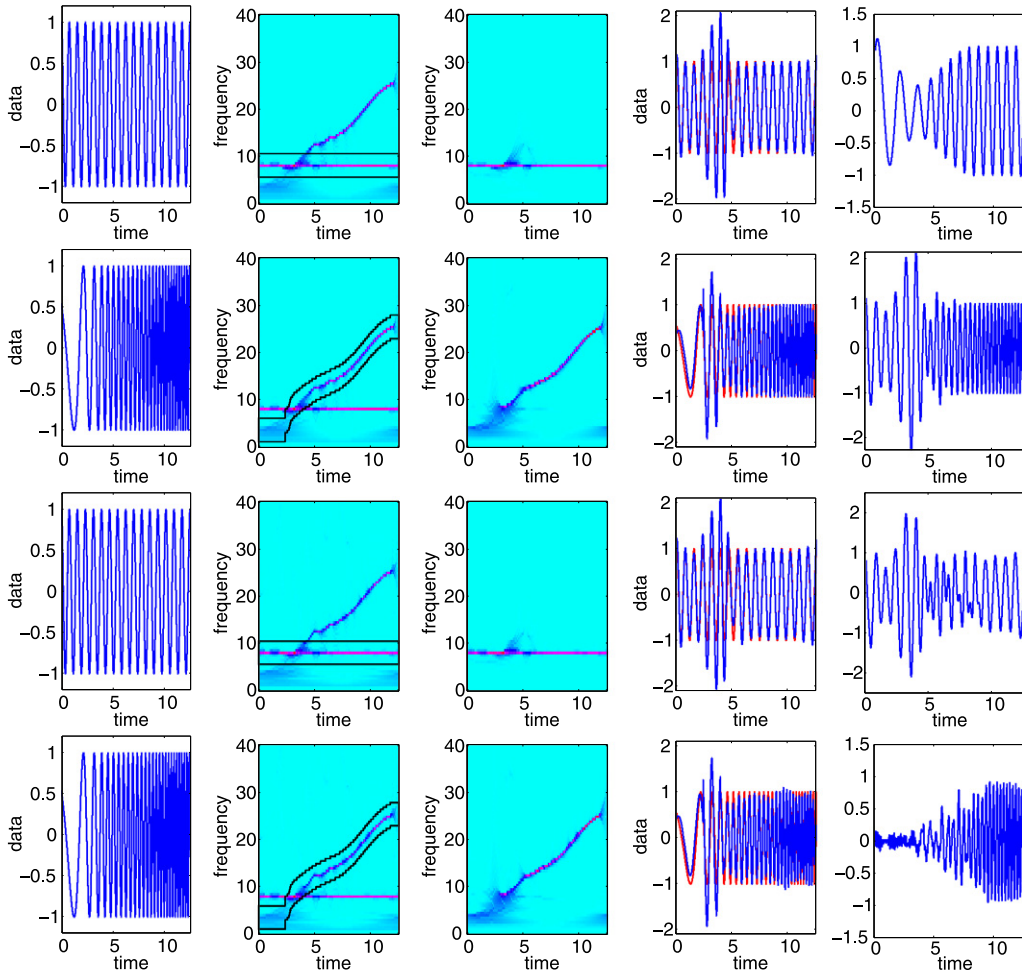


Fig. 9. Comparing the decomposition into components $s_1(t)$ and $s_2(t)$ of the crossover signal $s(t) = s_1(t) + s_2(t) = \cos(8t) + \cos[t^2 + t + \cos(t)]$. Rows: noise-free situation in the first two rows; in the last two rows noise with $\text{SNR} = 6.45$ dB was added to the mixed signal. In each case, s_1 is in the top row, and s_2 underneath. Columns: far left: true $s_j(t)$ $j = 1, 2$; middle left: zone marked on the synchrosqueezed transform for reconstruction of the component; center: part of the synchrosqueezed transform singled out for the reconstruction of a putative s_j ; middle right: the corresponding candidate $s_j(t)$ according to the synchrosqueezed transform (plotted in blue over the original s_j , in red); far right: candidate s_j according to EMD in the noiseless case, EEMD in the noisy case. (For interpretation of colors in this figure, the reader is referred to the web version of this article.)

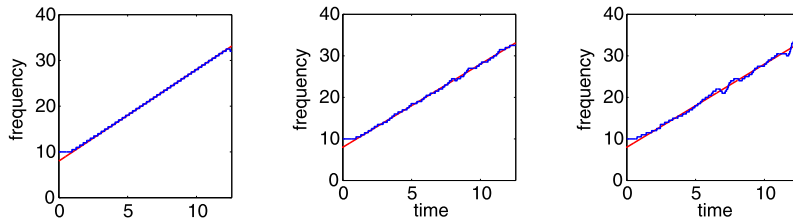


Fig. 10. Instantaneous frequency curves extracted from the synchrosqueezed representation. Left: the instantaneous frequency of the clean single chirp signal estimated by synchrosqueezing; middle: the instantaneous frequency of the fairly noisy single chirp signal ($\text{SNR} = -3.00$ dB) estimated by synchrosqueezing; right: the instantaneous frequency of the noisy single chirp signal ($\text{SNR} = -12.55$ dB) estimated by synchrosqueezing.

$\tilde{s}_i(t) = \sum_{\xi \geq \xi_{i, \text{cut-off}}} \mathcal{T}_{s_i}(t, \xi)$, with frequency cut-off $\xi_{i, \text{cut-off}}(t) = \omega_i(t) + \omega_0$, where $\omega_i(t)$ was the dominant component for signal i ($i = \ell$ or r) near 1 Hz with the highest frequency, and ω_0 a small constant offset. The right column in Fig. 11 shows the results; the erratic drift has disappeared and the peaks are well preserved.

5.3.2. Electrocardiogram data

In this application we use synchrosqueezing to extract the heart rate variability (HRV) from a real electrocardiogram (ECG) signal. The data was acquired from a resting healthy male with a portable ECG machine at sampling rate 1000 Hz for

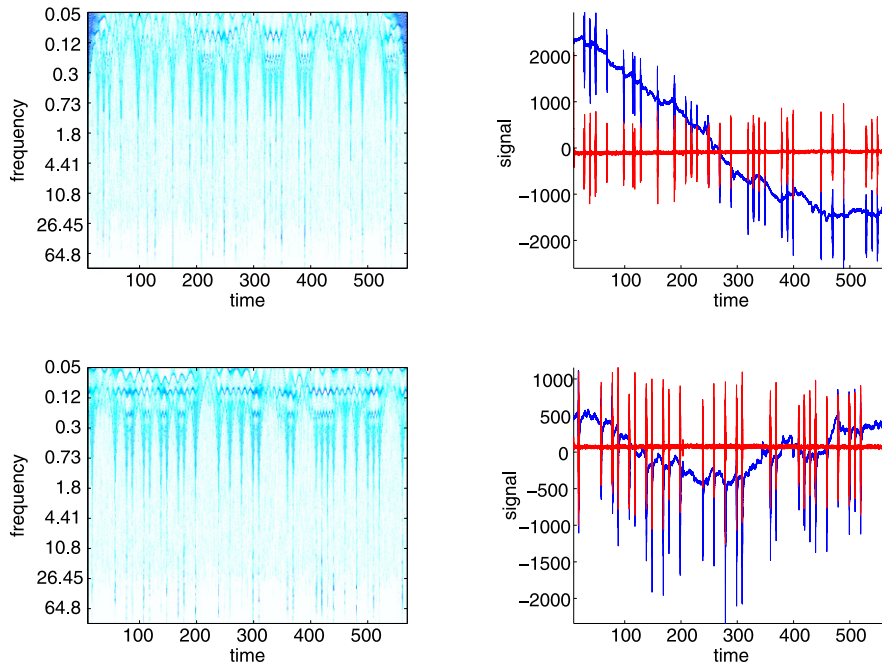


Fig. 11. The surface electromyography data described in the text. The erratic (and different) drifts present in these signals are pretty typical. The very short-lived peaks correspond to the elbow-flexes by the subject. Left column: the synchrosqueezing transforms of the surface electromyography signals. Coarse scales are near the top of these diagrams, finer scales are shown lower. The peaks are clearly marked over a range of fine scales. Right column: the red curve give the signals “sans drift”, reconstructed by deleting the low frequency region in the synchrosqueezed transforms; comparison with the original sEMG signals (in blue) shows the R peaks are as sharp as in the original signals, and at precisely the same location. (For interpretation of colors in this figure, the reader is referred to the web version of this article.)

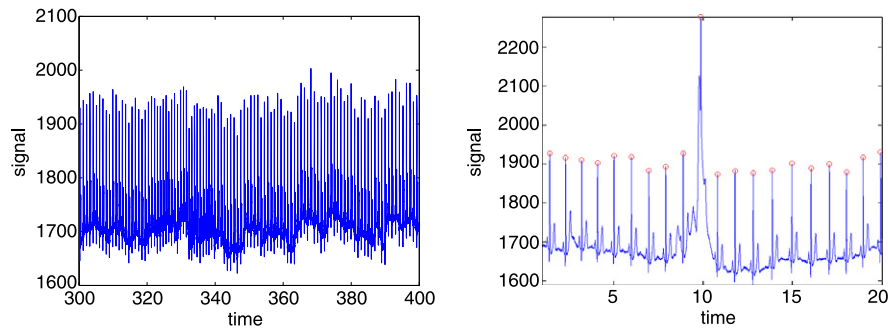


Fig. 12. The raw electrocardiogram data. Left: portion between 300 and 400 sec; right: blow-up of the stretch between 320 and 340 sec, with the R peaks marked.

600 seconds. The samples were quantized at 12 bits across ± 10 mV. The raw ECG data $e(t)$ are (partially) shown in the left half of Fig. 12; the right half of the figure shows a blow-up of 20 seconds of the same signal.

The strong, fairly regular spikes in the ECG are called the R peaks; the HRV time series is defined as the sequence of time differences between consecutive R peaks. (The interval between two consecutive R peaks is also called the RR interval.) The HRV is important for both clinical and basic research; it reflects the physiological dynamics and state of health of the subject. (See, e.g., [20] for clinical guidelines pertaining to the HRV, and [21] recent advances made in research.) The HRV can be viewed as a succession of snapshots of an averaged version of the instantaneous heart rate.

The left half of Fig. 13 shows the synchrosqueezed transform $T_e(\omega, t)$ of $e(t)$; in this case we used an implementation in which each dyadic scale interval ($a \in [2^k, 2^{k+1}]$) was divided into 128 equi-log-spaced bins. The synchrosqueezed transform $T_e(\omega, t)$ has a dominant line $c(t)$ near 1.2 Hz, the support of which can be parameterized as $\{(t, \omega_c(t)); t \in [0.80 \text{ sec}]\}$. The right half of Fig. 13 tracks the dependence on t of $\omega_c(t)$. This figure also plots a (piecewise constant) function $f(t)$ that tracks the HRV time series and that is computed as follows: if t lies between t_i and t_{i+1} , the locations in time for the i -th and $(i+1)$ -st R peaks, then $f(t) = [t_{i+1} - t_i]^{-1}$. The plot for $\omega_c(t)$ and $f(t)$ are clearly highly correlated.

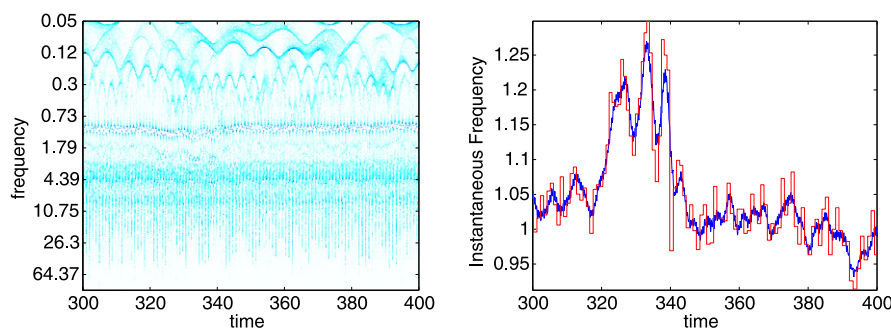


Fig. 13. Left: the synchrosqueezing transforms of the electrocardiogram signals given in Fig. 12. Right: the blue curve shows the “instantaneous heart rate” $\omega(t)$ computed by tracking the support of the dominant curve in the synchrosqueezed transform T_e ; the red curve is the (piecewise constant) inverse of the successive RR_i . (For interpretation of colors in this figure, the reader is referred to the web version of this article.)

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