



# LMZ10503 3-A SIMPLE SWITCHER® Power Module With 5.5-V Maximum Input Voltage

## 1 Features

- Integrated Shielded Inductor
- Flexible Start-up Sequencing Using External Soft-Start, Tracking, and Precision Enable
- Protection Against In-Rush Currents and Faults Such as Input UVLO and Output Short-Circuit
- Single Exposed Pad and Standard Pinout for Easy Mounting and Manufacturing
- Pin-to-Pin Compatible With
  - LMZ10504 (4 A / 20 W Maximum)
  - LMZ10505 (5 A / 25 W Maximum)
- Fully Enabled for WEBENCH® and Power Designer
- Electrical Specifications
  - 15-W Maximum Total Output Power
  - Up to 3-A Output Current
  - Input Voltage Range 2.95 V to 5.5 V
  - Output Voltage Range 0.8 V to 5 V
  - $\pm 1.63\%$  Feedback Voltage Accuracy Over Temperature
- Performance Benefits
  - Operates at High Ambient Temperatures
  - High Efficiency up to 96% Reduces System Heat Generation
  - Low Radiated Emissions (EMI) Tested to EN55022 Class B Standard
  - Fast Transient Response for Powering FPGAs and ASICs

NOTE: EN 55022:2006, +A1:2007, FCC Part 15 Subpart B: 2007. See [Table 9](#) and layout for information on device under test.

## 2 Applications

- Point-of-Load Conversions from 3.3-V and 5-V Rails
- Space-Constrained Applications
- Noise Sensitive Applications (that is, Transceiver, Medical)

## 3 Description

The LMZ10503 SIMPLE SWITCHER power module is a complete, easy-to-use DC-DC solution capable of driving up to a 3-A load with exceptional power conversion efficiency, output voltage accuracy, line and load regulation. The LMZ10503 is available in an innovative package that enhances thermal performance and allows for hand or machine soldering.

The LMZ10503 can accept an input voltage rail between 2.95 V and 5.5 V and can deliver an adjustable and highly accurate output voltage as low as 0.8 V. One megahertz fixed-frequency PWM switching provides a predictable EMI characteristic. Two external compensation components can be adjusted to set the fastest response time, while allowing the option to use ceramic and/or electrolytic output capacitors. Externally programmable soft-start capacitor facilitates controlled startup. The LMZ10503 is a reliable and robust solution with the following features: lossless cycle-by-cycle peak current limit to protect for over current or short-circuit fault, thermal shutdown, input undervoltage lockout, and prebiased start-up.

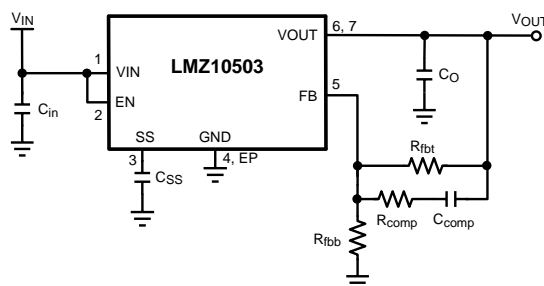
### Device Information<sup>(1)(2)</sup>

PART NUMBER	PACKAGE	BODY SIZE (NOM)
LMZ10503	TO-PMOD (7)	10.16 mm x 9.85 mm

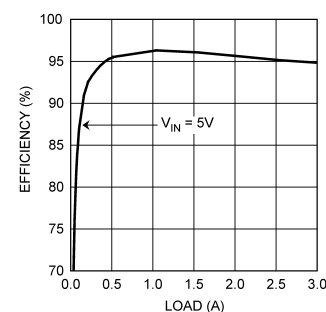
(1) For all available packages, see the orderable addendum at the end of the data sheet.

(2) Peak reflow temperature equals 245°C. See [SNAA214](#) for more details.

### Typical Application Circuit



### Efficiency $V_{OUT} = 3.3\text{ V}$



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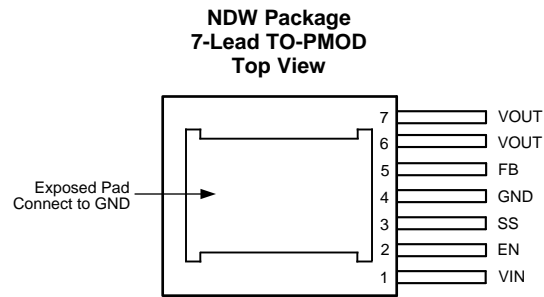
## 4 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

Changes from Revision I (October 2013) to Revision J	Page
• Added <i>Pin Configuration and Functions</i> section, <i>ESD Ratings</i> table, <i>Feature Description</i> section, <i>Device Functional Modes</i> , <i>Application and Implementation</i> section, <i>Power Supply Recommendations</i> section, <i>Layout</i> section, <i>Device and Documentation Support</i> section, and <i>Mechanical, Packaging, and Orderable Information</i> section	1
• Removed Easy-To-Use PFM 7-Pin Package image	1

Changes from Revision H (April 2013) to Revision I	Page
• Deleted 10 mils	4
• Changed 10 mils	23
• Added <i>Power Module SMT Guidelines</i>	27

## 5 Pin Configuration and Functions



### Pin Functions

PIN		TYPE	DESCRIPTION
NAME	NO.		
EN	2	Analog	Active-high enable input for the device.
Exposed Pad	—	Ground	Exposed pad is used as a thermal connection to remove heat from the device. Connect this pad to the PCB ground plane in order to reduce thermal resistance value. EP must also provide a direct electrical connection to the input and output capacitors ground terminals. Connect EP to pin 4.
FB	5	Analog	Feedback pin. This is the inverting input of the error amplifier used for sensing the output voltage. Keep the copper area of this node small.
GND	4	Ground	Power ground and signal ground. Provide a direct connection to the EP. Place the bottom feedback resistor as close as possible to GND and FB pin.
SS	3	Analog	Soft-start control pin. An internal 2-μA current source charges an external capacitor connected between SS and GND pins to set the output voltage ramp rate during startup. The SS pin can also be used to configure the tracking feature.
VIN	1	Power	Power supply input. A low ESR input capacitance should be located as close as possible to the VIN pin and exposed pad (EP).
VOUT	6, 7	Power	The output terminal of the internal inductor. Connect the output filter capacitor between VOUT pin and EP.

## 6 Specifications

### 6.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted)<sup>(1)(2)(3)</sup>

	MIN	MAX	UNIT
VIN, VOUT, EN, FB, SS to GND	−0.3	6	V
Power Dissipation	Internally Limited		
Junction Temperature		150	°C
Peak Reflow Case Temperature (30 sec)		245	°C
Storage Temperature, T <sub>stg</sub>	−65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) For soldering specifications, refer to the following document: [SNOA549](#)
- (3) If Military/Aerospace specified devices are required, please contact the Texas Instruments Sales Office/Distributors for availability and specifications.

### 6.2 ESD Ratings

	VALUE	UNIT
V <sub>(ESD)</sub> Electrostatic discharge Human body model (HBM) <sup>(1)</sup>	±2000	V

- (1) The human body model is a 100-pF capacitor discharged through a 1.5-kΩ resistor into each pin. Test method is per JESD22-A114S.

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### 6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

	MIN	MAX	UNIT
V <sub>IN</sub> to GND	2.95	5.5	V
Junction Temperature (T <sub>J</sub> )	–40	125	°C

### 6.4 Thermal Information

THERMAL METRIC <sup>(1)</sup>		LMZ10503	UNIT
		NDW (TO-PMOD)	
		7 PINS	
R <sub>θJA</sub>	Junction-to-ambient thermal resistance <sup>(2)</sup>	20	°C/W
R <sub>θJC(top)</sub>	Junction-to-case (top) thermal resistance	1.9	°C/W

- (1) For more information about traditional and new thermal metrics, see the *IC Package Thermal Metrics* application report, [SPRA953](#).  
(2) R<sub>θJA</sub> measured on a 2.25-in x 2.25-in (5.8 cm x 5.8 cm) 4-layer board, with 1-oz. copper, thirty six thermal vias, no air flow, and 1-W power dissipation. Refer to [Layout](#) or Evaluation Board Application Note: AN-2022 ([SNVA421](#)).

### 6.5 Electrical Characteristics

Specifications are for T<sub>J</sub> = 25°C unless otherwise specified. Minimum and maximum limits are ensured through test, design, or statistical correlation. Typical values represent the most likely parametric norm at T<sub>J</sub> = 25°C, and are provided for reference purposes only. V<sub>IN</sub> = V<sub>EN</sub> = 3.3 V, unless otherwise indicated in the conditions column.

PARAMETER		TEST CONDITIONS	MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
<b>SYSTEM PARAMETERS</b>						
V <sub>FB</sub>	Total Feedback Voltage Variation Including Line and Load Regulation	V <sub>IN</sub> = 2.95 V to 5.5 V V <sub>OUT</sub> = 2.5 V I <sub>OUT</sub> = 0 A to 3 A			0.8	V
			over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		0.78 0.82	
V <sub>FB</sub>	Feedback Voltage Variation	V <sub>IN</sub> = 3.3 V, V <sub>OUT</sub> = 2.5 V I <sub>OUT</sub> = 0 A			0.8	V
			over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		0.787 0.812	
V <sub>FB</sub>	Feedback Voltage Variation	V <sub>IN</sub> = 3.3 V, V <sub>OUT</sub> = 2.5 V I <sub>OUT</sub> = 3 A			0.798	V
			over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		0.785 0.81	
V <sub>IN(UVLO)</sub>	Input UVLO Threshold (Measured at VIN pin)	Rising			2.6	V
			over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		2.95	
		Falling			2.4	
			over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		1.95	
I <sub>SS</sub>	Soft-Start Current	Charging Current			2	μA
I <sub>Q</sub>	Non-Switching Input Current	V <sub>FB</sub> = 1 V			1.7	mA
			over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		3	
I <sub>SD</sub>	Shutdown Quiescent Current	V <sub>IN</sub> = 5.5 V, V <sub>EN</sub> = 0 V			260	μA
			over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		500	

- (1) Minimum and maximum limits are 100% production tested at an ambient temperature (T<sub>A</sub>) of 25°C. Limits over the operating temperature range are ensured through correlation using Statistical Quality Control (SQC) methods. Limits are used to calculate Average Outgoing Quality Level (AOQL).  
(2) Typical numbers are at 25°C and represent the most likely parametric norm.

## Electrical Characteristics (continued)

Specifications are for  $T_J = 25^\circ\text{C}$  unless otherwise specified. Minimum and maximum limits are ensured through test, design, or statistical correlation. Typical values represent the most likely parametric norm at  $T_J = 25^\circ\text{C}$ , and are provided for reference purposes only.  $V_{IN} = V_{EN} = 3.3\text{ V}$ , unless otherwise indicated in the conditions column.

PARAMETER		TEST CONDITIONS		MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
I <sub>OCL</sub>	Output Current Limit (Average Current)	V <sub>OUT</sub> = 2.5 V	over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C	3.8	5.2	6.7	A
f <sub>FB</sub>	Frequency Fold-back	In current limit			250		kHz
PWM SECTION							
f <sub>SW</sub>	Switching Frequency		over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C	750	1000	1160	kHz
D <sub>range</sub>	PWM Duty Cycle Range	over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C			0%	100%	
ENABLE CONTROL							
V <sub>EN-IH</sub>	EN Pin Rising Threshold		over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		1.23	1.8	V
V <sub>EN-IF</sub>	EN Pin Falling Threshold		over the operating junction temperature range T <sub>J</sub> of –40°C to 125°C		1.06	0.8	V
THERMAL CONTROL							
T <sub>SD</sub>	T <sub>J</sub> for Thermal Shutdown				145		°C
T <sub>SD-HYS</sub>	Hysteresis for Thermal Shutdown				10		°C
PERFORMANCE PARAMETERS							
ΔV <sub>OUT</sub>	Output Voltage Ripple	Refer to <a href="#">Table 1</a> V <sub>OUT</sub> = 2.5 V Bandwidth Limit = 2 MHz			7		mV <sub>pk-pk</sub>
ΔV <sub>OUT</sub>	Output Voltage Ripple	Refer to <a href="#">Table 5</a> Bandwidth Limit = 20 MHz			5		mV <sub>pk-pk</sub>
ΔV <sub>FB</sub> / V <sub>FB</sub>	Feedback Voltage Line Regulation	ΔV <sub>IN</sub> = 2.95 V to 5.5 V I <sub>OUT</sub> = 0 A			0.04%		
ΔV <sub>OUT</sub> / V <sub>OUT</sub>	Output Voltage Line Regulation	ΔV <sub>IN</sub> = 2.95 V to 5.5 V I <sub>OUT</sub> = 0 A, V <sub>OUT</sub> = 2.5 V			0.04%		
ΔV <sub>FB</sub> / V <sub>FB</sub>	Feedback Voltage Load Regulation	I <sub>OUT</sub> = 0 A to 3 A			0.25%		
ΔV <sub>OUT</sub> / V <sub>OUT</sub>	Output Voltage Load Regulation	I <sub>OUT</sub> = 0 A to 3 A V <sub>OUT</sub> = 2.5 V			0.25%		
Efficiency							
η	Peak Efficiency (1 A) V <sub>IN</sub> = 5 V	V <sub>OUT</sub> = 3.3 V			96.3%		
		V <sub>OUT</sub> = 2.5 V			94.9%		
		V <sub>OUT</sub> = 1.8 V			93.3%		
		V <sub>OUT</sub> = 1.5 V			92.2%		
		V <sub>OUT</sub> = 1.2 V			90.5%		
		V <sub>OUT</sub> = 0.8 V			86.9%		
η	Peak Efficiency (1 A) V <sub>IN</sub> = 3.3 V	V <sub>OUT</sub> = 2.5 V			95.7%		
		V <sub>OUT</sub> = 1.8 V			94%		
		V <sub>OUT</sub> = 1.5 V			92.9%		
		V <sub>OUT</sub> = 1.2 V			91.3%		
		V <sub>OUT</sub> = 0.8 V			87.9%		

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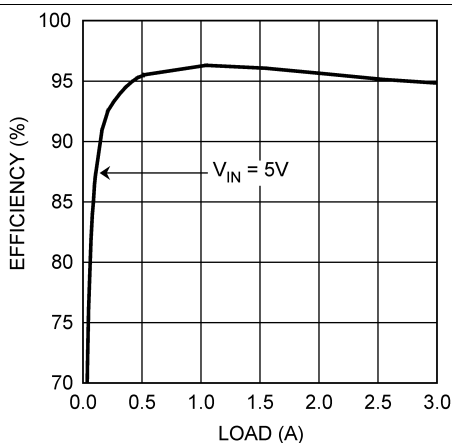
### Electrical Characteristics (continued)

Specifications are for  $T_J = 25^\circ\text{C}$  unless otherwise specified. Minimum and maximum limits are ensured through test, design, or statistical correlation. Typical values represent the most likely parametric norm at  $T_J = 25^\circ\text{C}$ , and are provided for reference purposes only.  $V_{IN} = V_{EN} = 3.3\text{ V}$ , unless otherwise indicated in the conditions column.

PARAMETER	TEST CONDITIONS	MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
$\eta$ Full Load Efficiency (3 A) $V_{IN} = 5\text{ V}$	$V_{OUT} = 3.3\text{ V}$		94.8%		
	$V_{OUT} = 2.5\text{ V}$		93%		
	$V_{OUT} = 1.8\text{ V}$		90.8%		
	$V_{OUT} = 1.5\text{ V}$		89.3%		
	$V_{OUT} = 1.2\text{ V}$		87.1%		
	$V_{OUT} = 0.8\text{ V}$		82.3%		
$\eta$ Full Load Efficiency (3 A) $V_{IN} = 3.3\text{ V}$	$V_{OUT} = 2.5\text{ V}$		92.4%		
	$V_{OUT} = 1.8\text{ V}$		89.8%		
	$V_{OUT} = 1.5\text{ V}$		88.2%		
	$V_{OUT} = 1.2\text{ V}$		85.9%		
	$V_{OUT} = 0.8\text{ V}$		80.8%		

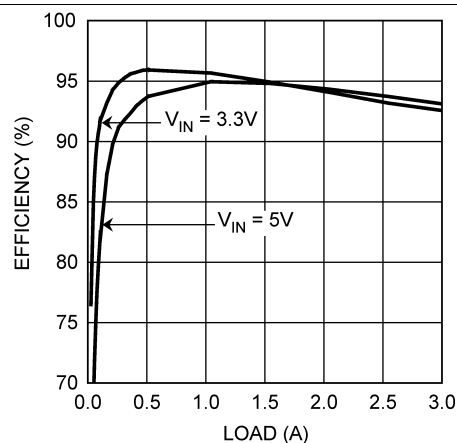
## 6.6 Typical Characteristics

Unless otherwise specified, the following conditions apply:  $V_{IN} = V_{EN} = 5\text{ V}$ ,  $C_{IN}$  is 47  $\mu\text{F}$  10-V X5R ceramic capacitor;  $T_A = 25^\circ\text{C}$  for efficiency curves and waveforms.



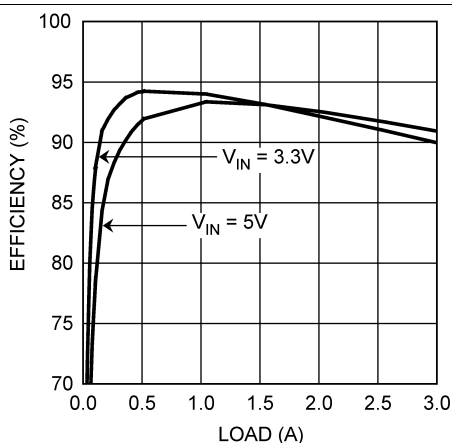
$V_{OUT} = 3.3\text{ V}$

**Figure 1. Efficiency**



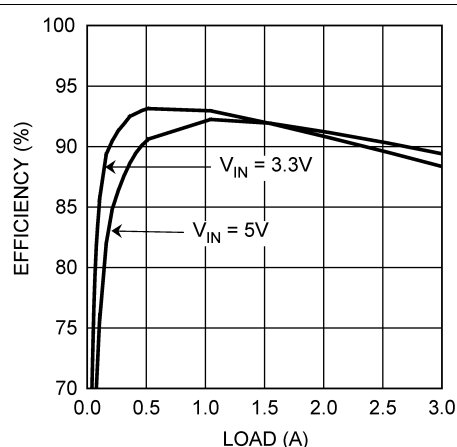
$V_{OUT} = 2.5\text{ V}$

**Figure 2. Efficiency**



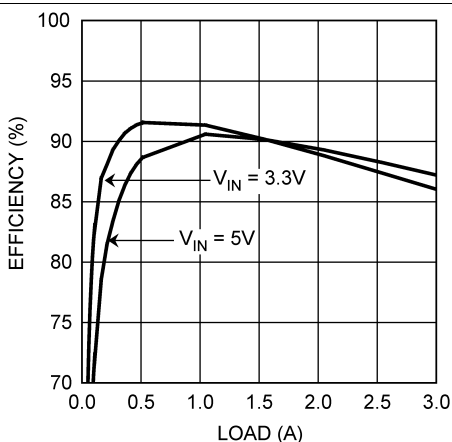
$V_{OUT} = 1.8\text{ V}$

**Figure 3. Efficiency**



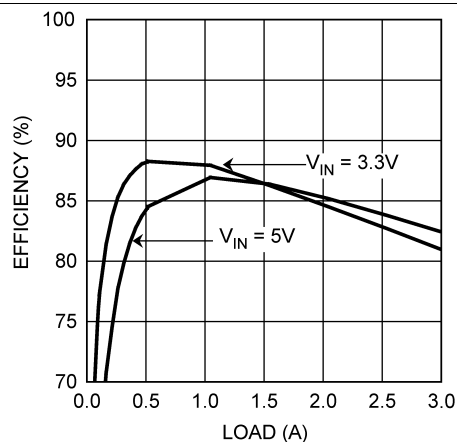
$V_{OUT} = 1.5\text{ V}$

**Figure 4. Efficiency**



$V_{OUT} = 1.2\text{ V}$

**Figure 5. Efficiency**

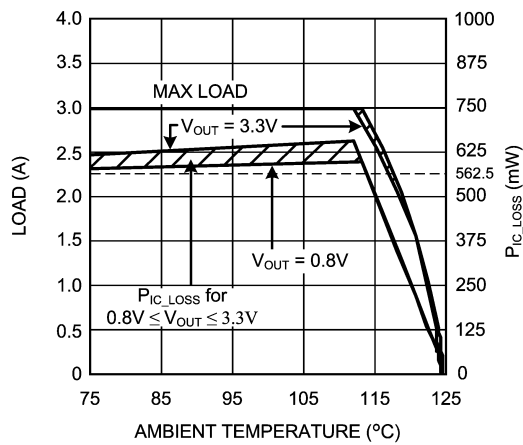


$V_{OUT} = 0.8\text{ V}$

**Figure 6. Efficiency**

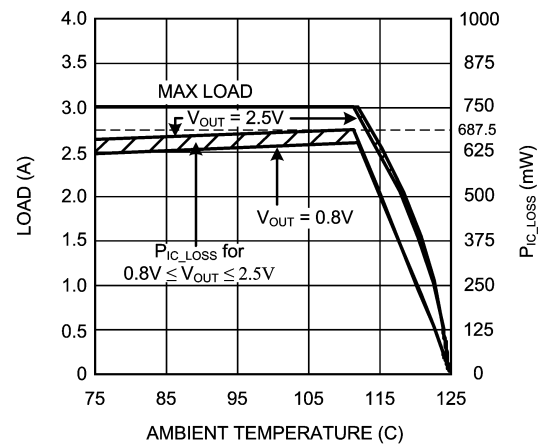
## Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply:  $V_{IN} = V_{EN} = 5\text{ V}$ ,  $C_{IN}$  is 47  $\mu\text{F}$  10-V X5R ceramic capacitor;  $T_A = 25^\circ\text{C}$  for efficiency curves and waveforms.



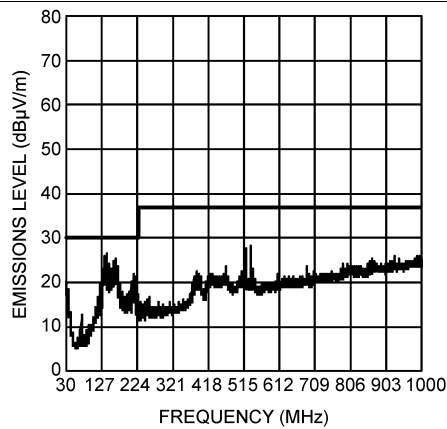
$V_{IN} = 5\text{ V}$ ,  $R_{\theta JA} = 20^\circ\text{C/W}$

**Figure 7. Current Derating**



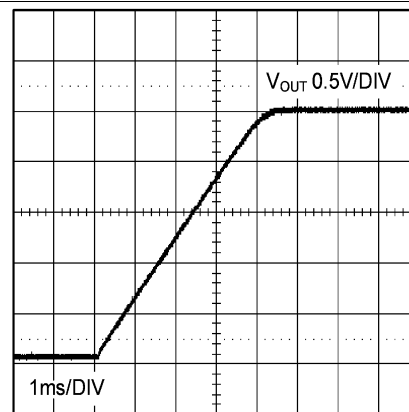
$V_{IN} = 3.3\text{ V}$ ,  $R_{\theta JA} = 20^\circ\text{C/W}$

**Figure 8. Current Derating**



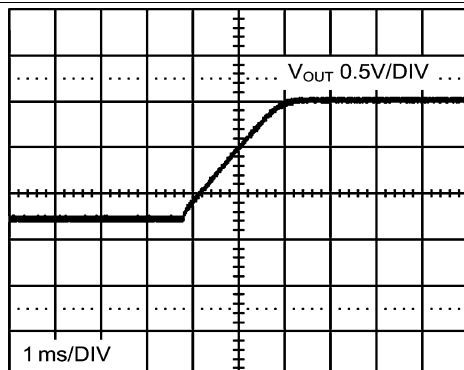
$V_{IN} = 5\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 3\text{ A}$

**Figure 9. Radiated Emissions (EN55022, Class B) Evaluation Board**



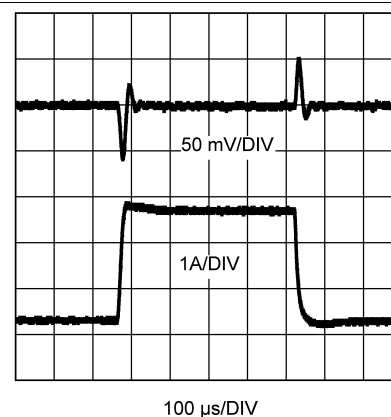
$V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 0\text{ A}$

**Figure 10. Start-Up**



$V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 0\text{ A}$

**Figure 11. Prebiased Start-Up**



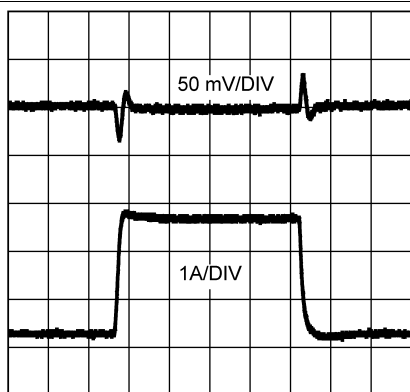
$V_{IN} = 3.3\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 0.3\text{ A}$  to  $2.7\text{ A}$  to  $0.3\text{ A}$  Step 20-MHz Bandwidth Limited. Refer to Table 5 for BOM, includes optional components

**Figure 12. Load Transient Response**



## Typical Characteristics (continued)

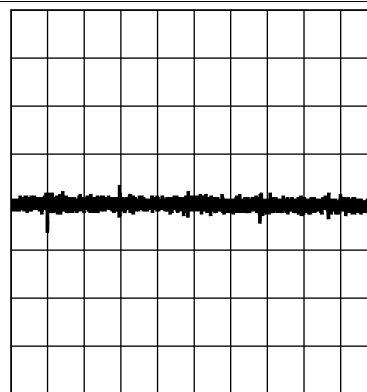
Unless otherwise specified, the following conditions apply:  $V_{IN} = V_{EN} = 5\text{ V}$ ,  $C_{IN}$  is 47  $\mu\text{F}$  10-V X5R ceramic capacitor;  $T_A = 25^\circ\text{C}$  for efficiency curves and waveforms.



100  $\mu\text{s}/\text{DIV}$

$V_{IN} = 5.0\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 0.3\text{ A}$  to  $2.7\text{ A}$  to  $0.3\text{-A}$  step  
20-MHz Bandwidth Limited. Refer to [Table 5](#) for BOM, includes  
optional components

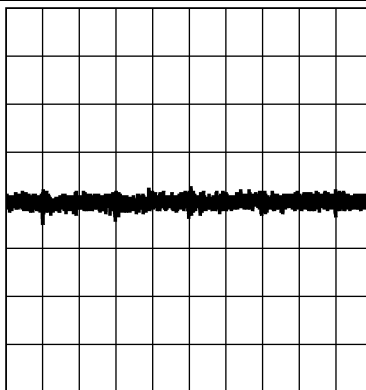
**Figure 13. Load Transient Response**



500 ns/DIV

$V_{IN} = 3.3\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 3\text{ A}$ ,  
20 mV/DIV. Refer to [Table 5](#) for BOM

**Figure 14. Output Voltage Ripple**



500 ns/DIV

$V_{IN} = 5\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 3\text{ A}$ ,  
20 mV/DIV. Refer to [Table 5](#) for BOM

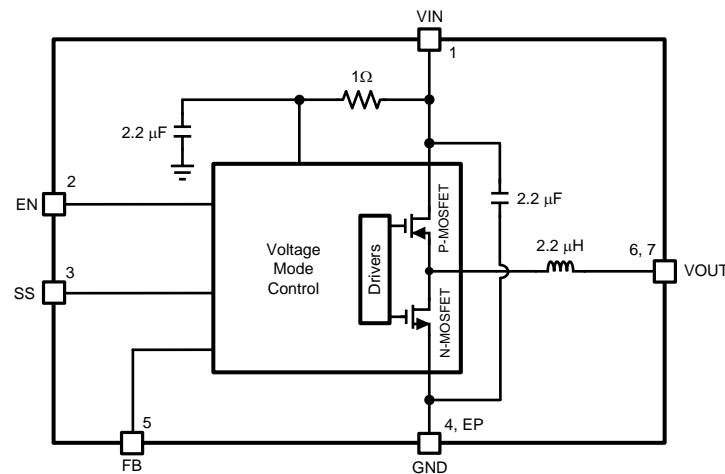
**Figure 15. Output Voltage Ripple**

## 7 Detailed Description

### 7.1 Overview

The LMZ10503 SIMPLE SWITCHER power module is a complete, easy-to-use DC-DC solution capable of driving up to a 3-A load with exceptional power conversion efficiency, output voltage accuracy, line and load regulation. The LMZ10503 is available in an innovative package that enhances thermal performance and allows for hand or machine soldering. The LMZ10503 is a reliable and robust solution with the following features: lossless cycle-by-cycle peak current limit to protect for overcurrent or short-circuit fault, thermal shutdown, input undervoltage lockout, and prebiased start-up.

### 7.2 Functional Block Diagram



### 7.3 Feature Description

#### 7.3.1 Enable

The LMZ10503 features an enable (EN) pin and associated comparator to allow the user to easily sequence the LMZ10503 from an external voltage rail, or to manually set the input UVLO threshold. The turnon or rising threshold and hysteresis for this comparator are typically 1.23 V and 0.15 V respectively. The precise reference for the enable comparator allows the user to ensure that the LMZ10503 will be disabled when the system demands it to be.

The EN pin should not be left floating. For always-on operation, connect EN to VIN.

#### 7.3.2 Enable and UVLO

Using a resistor divider from VIN to EN as shown in the schematic diagram below, the input voltage at which the part begins switching can be increased above the normal input UVLO level according to

$$V_{IN(ULVO)} = 1.23V \times \frac{R_{trkb} \times R_{trkt}}{R_{trkt}} \quad (1)$$

For example, suppose that the required input UVLO level is 3.69 V. Choosing  $R_{enb} = 10 \text{ k}\Omega$ , then we calculate  $R_{ent} = 20 \text{ k}\Omega$ .

## Feature Description (continued)

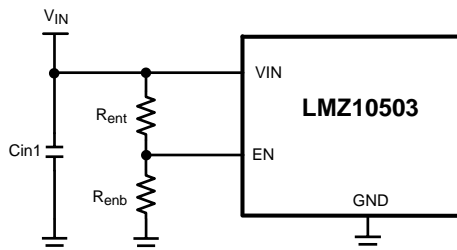


Figure 16. Setting Enable and UVLO

Alternatively, the EN pin can be driven from another voltage source to cater to system sequencing requirements commonly found in FPGA and other multi-rail applications. Figure 17 shows an LMZ10503 that is sequenced to start based on the voltage level of a master system rail ( $V_{OUT1}$ ).

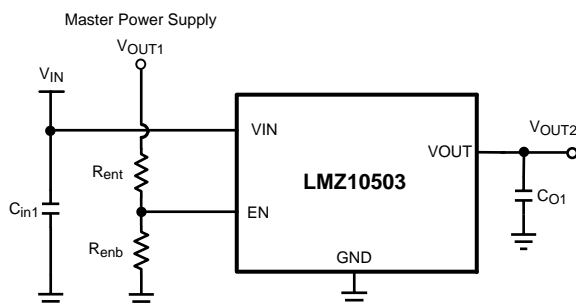


Figure 17. Setting Enable and UVLO Using External Power Supply

### 7.3.3 Soft-Start

The LMZ10503 begins to operate when both the VIN and EN, voltages exceed the rising UVLO and enable thresholds, respectively. A controlled soft-start eliminates inrush currents during start-up and allows the user more control and flexibility when sequencing the LMZ10503 with other power supplies.

In the event of either VIN or EN decreasing below the falling UVLO or enable threshold respectively, the voltage on the soft-start pin is collapsed by discharging the soft-start capacitor by a 14- $\mu$ A (typical) current sink to ground.

### 7.3.4 Soft-Start Capacitor

Determine the soft-start capacitance with the following relationship:

$$C_{SS} = \frac{t_{ss} \times I_{ss}}{V_{FB}}$$

where

- $V_{FB}$  is the internal reference voltage (nominally 0.8 V),  $I_{ss}$  is the soft-start charging current (nominally 2  $\mu$ A) and  $C_{SS}$  is the external soft-start capacitance. (2)

Thus, the required soft-start capacitor per unit output voltage startup time is given by:

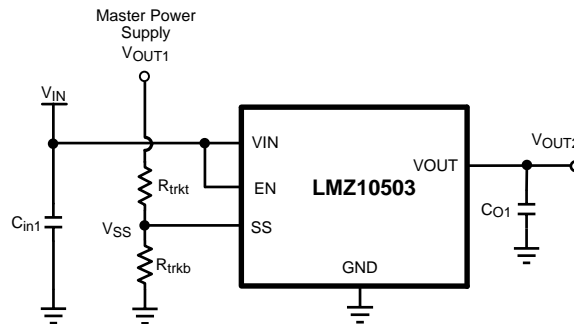
$$C_{SS} = 2.5 \text{ nF} / \text{ms} \quad (3)$$

For example, a 4-ms soft-start time will yield a 10-nF capacitance. The minimum soft-start capacitance is 680 pF.

## Feature Description (continued)

### 7.3.5 Tracking

The LMZ10503 can track the output of a master power supply during soft-start by connecting a resistor divider to the SS pin. In this way, the output voltage slew rate of the LMZ10503 will be controlled by a master supply for loads that require precise sequencing. When the tracking function is used, a small value soft-start capacitor should be connected to the SS pin to alleviate output voltage overshoot when recovering from a current limit fault.



**Figure 18. Tracking Using External Power Supply**

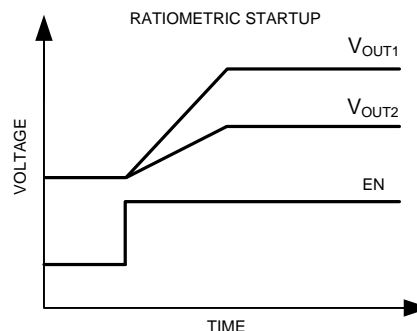
### 7.3.6 Tracking - Equal Soft-Start Time

One way to use the tracking feature is to design the tracking resistor divider so that the master supply output voltage,  $V_{OUT1}$ , and the LMZ10503 output voltage,  $V_{OUT2}$ , both rise together and reach their target values at the same time. This is termed ratiometric start-up. For this case, the equation governing the values of tracking divider resistors  $R_{trkb}$  and  $R_{trkt}$  is given by:

$$R_{trkb} = \frac{R_{trkt}}{V_{OUT1} - 1.0V} \quad (4)$$

Equation 4 includes an offset voltage, of 200 mV, to ensure that the final value of the SS pin voltage exceeds the reference voltage of the LMZ10503. This offset will cause the LMZ10503 output voltage to reach regulation slightly before the master supply. A value of 33 kΩ 1% is recommended for  $R_{trkt}$  as a compromise between high precision and low quiescent current through the divider while minimizing the effect of the 2-μA soft-start current source.

For example, if the master supply voltage  $V_{OUT1}$  is 3.3 V and the LMZ10503 output voltage was 1.8 V, then the value of  $R_{trkb}$  needed to give the two supplies identical soft-start times would be 14.3 kΩ. Figure 19 shows an example of tracking using the equal soft-start time.



**Figure 19. Timing Diagram for Tracking Using Equal Soft-Start Time**

### 7.3.7 Tracking - Equal Slew Rates

Alternatively, the tracking feature can be used to have similar output voltage ramp rates. This is referred to as simultaneous start-up. In this case, the tracking resistors can be determined based on Equation 5:

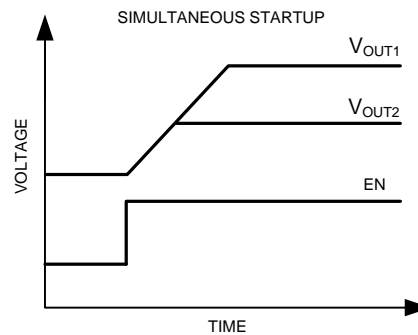
## Feature Description (continued)

$$R_{trkb} = \frac{0.8V}{V_{OUT2} - 0.8V} \times R_{trkt} \quad (5)$$

and to ensure proper overdrive of the SS pin:

$$V_{OUT2} < 0.8 \times V_{OUT1} \quad (6)$$

For the example case of  $V_{OUT1} = 5\text{ V}$  and  $V_{OUT2} = 2.5\text{ V}$ , with  $R_{trkt}$  set to  $33\text{ k}\Omega$  as before,  $R_{trkb}$  is calculated from the above equation to be  $15.5\text{ k}\Omega$ . Figure 20 shows an example of tracking using the equal slew rates.



**Figure 20. Timing Diagram for Tracking Using Equal Slew Rates**

### 7.3.8 Current Limit

When a current greater than the output current limit ( $I_{OCL}$ ) is sensed, the ON-time is immediately terminated and the low-side MOSFET is activated. The low-side MOSFET stays on for the entire next four switching cycles. During these skipped pulses, the voltage on the soft-start pin is reduced by discharging the soft-start capacitor by a current sink on the soft-start pin of nominally  $14\text{ }\mu\text{A}$ . Subsequent overcurrent events will drain more and more charge from the soft-start capacitor, effectively decreasing the reference voltage as the output droops due to the pulse skipping. Reactivation of the soft-start circuitry ensures that when the overcurrent situation is removed, the part will resume normal operation smoothly.

### 7.3.9 Overtemperature Protection

When the LMZ10503 senses a junction temperature greater than  $145^{\circ}\text{C}$  (typical), both switching MOSFETs are turned off and the part enters a standby state. Upon sensing a junction temperature below  $135^{\circ}\text{C}$  (typical), the part will re-initiate the soft-start sequence and begin switching once again.

## 7.4 Device Functional Modes

### 7.4.1 Prebias Start-Up Capability

At start-up, the LMZ10503 is in a prebiased state when the output voltage is greater than zero. This often occurs in many multi-rail applications such as when powering an ASIC, FPGA, or DSP. The output can be prebiased in these applications through parasitic conduction paths from one supply rail to another. Even though the LMZ10503 is a synchronous converter, it will not pull the output low when a prebias condition exists. The LMZ10503 will not sink current during start-up until the soft-start voltage exceeds the voltage on the FB pin. Because the device does not sink current it protects the load from damage that might otherwise occur if current is conducted through the parasitic paths of the load.

## 8 Application and Implementation

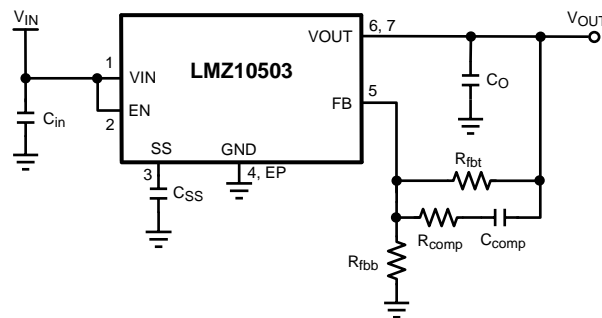
### NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

### 8.1 Application Information

The LMZ10503 is a step-down DC-to-DC power module. It is typically used to convert a higher DC voltage to a lower DC voltage with a maximum output current of 3 A. The following design procedure can be used to select components for the LMZ10503. Alternately, the WEBENCH software may be used to generate complete designs. When generating a design, the WEBENCH software uses iterative design procedure and accesses comprehensive databases of components. Please go to [www.ti.com](http://www.ti.com) for more details.

### 8.2 Typical Application



**Figure 21. Typical Application Circuit**

#### 8.2.1 Design Requirements

For this example the following application parameters exist.

- $V_{IN} = 5\text{ V}$
- $V_{OUT} = 2.5\text{ V}$
- $I_{OUT} = 3\text{ A}$
- $\Delta V_{OUT} = 20\text{ mV}_{pk-pk}$
- $\Delta V_{o\_tran} = \pm 20\text{ mV}_{pk-pk}$

**Table 1. Bill of Materials,  $V_{IN} = 3.3\text{ V}$  to  $5\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT (MAX)} = 3\text{ A}$ , Optimized for Electrolytic Input and Output Capacitance**

DESIGNATOR	DESCRIPTION	CASE SIZE	MANUFACTURER	MANUFACTURER P/N	QUANTITY
U1	SIMPLE SWITCHER	PFM-7	Texas Instruments	LMZ10503	1
C <sub>in1</sub>	150 $\mu\text{F}$ , 6.3 V, 18 m $\Omega$	C2, 6.0 x 3.2 x 1.8 mm	Sanyo	6TPE150MIC2	1
C <sub>O1</sub>	330 $\mu\text{F}$ , 6.3 V, 18 m $\Omega$	D3L, 7.3 x 4.3 x 2.8 mm	Sanyo	6TPE330MIL	1
R <sub>fbt</sub>	100 k $\Omega$	0603	Vishay Dale	CRCW0603100KFKEA	1
R <sub>fbb</sub>	47.5 k $\Omega$	0603	Vishay Dale	CRCW060347K5FKEA	1
R <sub>comp</sub>	15 k $\Omega$	0603	Vishay Dale	CRCW060315K0FKEA	1
C <sub>comp</sub>	330 pF, $\pm 5\%$ , C0G, 50 V	0603	TDK	C1608C0G1H331J	1
C <sub>SS</sub>	10 nF, $\pm 10\%$ , X7R, 16 V	0603	Murata	GRM188R71C103KA01	1

**Table 2. Bill of Materials,  $V_{IN} = 3.3\text{ V}$ ,  $V_{OUT} = 0.8\text{ V}$ ,  $I_{OUT (MAX)} = 3\text{ A}$ , Optimized for Solution Size and Transient Response**

DESIGNATOR	DESCRIPTION	CASE SIZE	MANUFACTURER	MANUFACTURER P/N	QUANTITY
U1	SIMPLE SWITCHER	PFM-7	Texas Instruments	LMZ10503TZ	1
$C_{in1}$ , $C_{O1}$	47 $\mu\text{F}$ , X5R, 6.3 V	1206	TDK	C3216X5R0J476M	2
$R_{fbt}$	110 k $\Omega$	0402	Vishay Dale	CRCW0402100KFKED	1
$R_{comp}$	1.0 k $\Omega$	0402	Vishay Dale	CRCW04021K00FKED	1
$C_{comp}$	27 pF, $\pm 5\%$ , C0G, 50 V	0402	Murata	GRM1555C1H270JZ01	1
$C_{SS}$	10 nF, $\pm 10\%$ , X7R, 16 V	0402	Murata	GRM155R71C103KA01	1

## 8.2.2 Detailed Design Procedure

LMZ10503 is fully supported by WEBENCH and offers the following: component selection, performance, electrical, and thermal simulations as well as the Build-It board, for a reduced design time. On the other hand, all external components can be calculated by following the design procedure below.

1. Determine the input voltage and output voltage. Also, make note of the ripple voltage and voltage transient requirements.
2. Determine the necessary input and output capacitance.
3. Calculate the feedback resistor divider.
4. Select the optimized compensation component values.
5. Estimate the power dissipation and board thermal requirements.
6. Follow the PCB design guideline.
7. Learn about the LMZ10503 features such as enable, input UVLO, soft-start, tracking, prebiased start-up, current limit, and thermal shutdown.

### 8.2.2.1 Input Capacitor Selection

A 22- $\mu\text{F}$  or 47- $\mu\text{F}$ , high-quality dielectric (X5R, X7R) ceramic capacitor rated at twice the maximum input voltage is typically sufficient. The input capacitor must be placed as close as possible to the  $V_{IN}$  pin and GND exposed pad to substantially eliminate the parasitic effects of any stray inductance or resistance on the PCB and supply lines.

Neglecting capacitor equivalent series resistance (ESR), the resultant input capacitor AC ripple voltage is a triangular waveform. The minimum input capacitance for a given peak-to-peak value ( $\Delta V_{IN}$ ) of  $V_{IN}$  is specified as follows:

$$C_{in} \geq \frac{I_{OUT} \times D \times (1-D)}{f_{SW} \times \Delta V_{IN}}$$

where

- the PWM duty cycle,  $D$ , is given by [Equation 8](#):

$$D = \frac{V_{OUT}}{V_{IN}} \quad (8)$$

If  $\Delta V_{IN}$  is 1% of  $V_{IN}$ , this equals to 50 mV and  $f_{SW} = 1\text{ MHz}$ .

$$C_{in} \geq \frac{3\text{ A} \times \left(\frac{2.5\text{ V}}{5\text{ V}}\right) \times \left(1 - \frac{2.5\text{ V}}{5\text{ V}}\right)}{1\text{ MHz} \times 50\text{ mV}} \geq 15\text{ }\mu\text{F} \quad (9)$$

A second criteria before finalizing the  $C_{in}$  bypass capacitor is the RMS current capability. The necessary RMS current rating of the input capacitor to a buck regulator can be estimated by:

$$I_{Cin(RMS)} = I_{OUT} \times \sqrt{D(1-D)} \quad (10)$$

$$I_{Cin(RMS)} = 3\text{ A} \times \sqrt{\frac{2.5\text{ V}}{5\text{ V}} \left(1 - \frac{2.5\text{ V}}{5\text{ V}}\right)} = 1.5\text{ A} \quad (11)$$

With this high AC current present in the input capacitor, the RMS current rating becomes an important parameter. The maximum input capacitor ripple voltage and RMS current occur at 50% duty cycle. Select an input capacitor rated for at least the maximum calculated  $I_{Cin(RMS)}$ .

Additional bulk capacitance with higher ESR may be required to damp any resonance effects of the input capacitance and parasitic inductance.

### 8.2.2.2 Output Capacitor Selection

In general, 22- $\mu$ F to 100- $\mu$ F, high-quality dielectric (X5R, X7R) ceramic capacitor rated at twice the maximum output voltage is sufficient given the optimal high-frequency characteristics and low ESR of ceramic dielectrics. Although, the output capacitor can also be of electrolytic chemistry for increased capacitance density.

Two output capacitance equations are required to determine the minimum output capacitance. One equation determines the output capacitance ( $C_O$ ) based on PWM ripple voltage. The second equation determines  $C_O$  based on the load transient characteristics. Select the largest capacitance value of the two.

The minimum capacitance, given the maximum output voltage ripple ( $\Delta V_{OUT}$ ) requirement, is determined by Equation 12:

$$C_O \geq \frac{\Delta i_L}{8 \times f_{sw} \times [\Delta V_{OUT} - (\Delta i_L \times R_{ESR})]}$$

where

- the peak to peak inductor current ripple ( $\Delta i_L$ ) is equal to Equation 13: (12)

$$\Delta i_L = \frac{(V_{IN} - V_{OUT}) \times D}{L \times f_{sw}} \quad (13)$$

$R_{ESR}$  is the total output capacitor ESR,  $L$  is the inductance value of the internal power inductor, where  $L = 2.2 \mu$ H, and  $f_{sw} = 1$  MHz. Therefore, per the design example:

$$\Delta i_L = \frac{(5V - 2.2V) \times \frac{2.5V}{5V}}{2.2 \mu H \times 1 MHz} = 568 mA \quad (14)$$

The minimum output capacitance requirement due to the PWM ripple voltage is:

$$C_O \geq \frac{568 mA}{8 \times 1 MHz \times [20 mV - (568 mA \times 3 m\Omega)]} \quad (15)$$

$$C_O \geq 4 \mu F \quad (16)$$

Three m $\Omega$  is a typical  $R_{ESR}$  value for ceramic capacitors.

Equation 17 provides a good first pass capacitance requirement for a load transient:

$$C_O \geq \frac{I_{step} \times V_{FB} \times L \times V_{IN}}{4 \times V_{OUT} \times (V_{IN} - V_{OUT}) \times \Delta V_{o\_tran}}$$

where

- $I_{step}$  is the peak to peak load step (for this example  $I_{step} = 10\%$  to  $90\%$  of the maximum load)
- $V_{FB} = 0.8 V$
- and  $\Delta V_{o\_tran}$  is the maximum output voltage deviation, which is  $\pm 20 mV$ . (17)

Therefore the capacitance requirement for the given design parameters is:

$$C_O \geq \frac{2.4A \times 0.8V \times 2.2 \mu H \times 5V}{4 \times 2.5V \times (5V - 2.5V) \times 20 mV} \quad (18)$$

$$C_O \geq 42 \mu F \quad (19)$$

In this particular design the output capacitance is determined by the load transient requirements.



Table 3 lists some examples of commercially available capacitors that can be used with the LMZ10503.

**Table 3. Recommended Output Filter Capacitors**

C <sub>O</sub> (μF)	VOLTAGE (V), R <sub>ESR</sub> (mΩ)	MAKE	MANUFACTURER	PART NUMBER	CASE SIZE
22	6.3, < 5	Ceramic, X5R	TDK	C3216X5R0J226M	1206
47	6.3, < 5	Ceramic, X5R	TDK	C3216X5R0J476M	1206
47	6.3, < 5	Ceramic, X5R	TDK	C3225X5R0J476M	1210
47	10.0, < 5	Ceramic, X5R	TDK	C3225X5R1A476M	1210
100	6.3, < 5	Ceramic, X5R	TDK	C3225X5R0J107M	1210
100	6.3, 50	Tantalum	AVX	TPSD157M006#0050	D, 7.5 x 4.3 x 2.9 mm
100	6.3, 25	Organic Polymer	Sanyo	6TPE100MPB2	B2, 3.5 x 2.8 x 1.9 mm
150	6.3, 18	Organic Polymer	Sanyo	6TPE150MIC2	C2, 6.0 x 3.2 x 1.8 mm
330	6.3, 18	Organic Polymer	Sanyo	6TPE330MIL	D3L, 7.3 x 4.3 x 2.8 mm
470	6.3, 23	Niobium Oxide	AVX	NOME37M006#0023	E, 7.3 x 4.3 x 4.1 mm

#### 8.2.2.2.1 Output Voltage Setting

A resistor divider network from V<sub>OUT</sub> to the FB pin determines the desired output voltage as follows:

$$V_{OUT} = 0.8V \times \frac{R_{fbt} + R_{fbb}}{R_{fbb}} \quad (20)$$

R<sub>fbt</sub> is defined based on the voltage loop requirements and R<sub>fbb</sub> is then selected for the desired output voltage. Resistors are normally selected as 0.5% or 1% tolerance. Higher accuracy resistors such as 0.1% are also available.

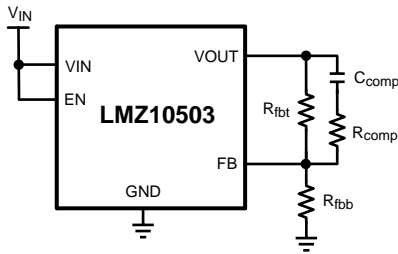
The feedback voltage (at V<sub>OUT</sub> = 2.5 V) is accurate to within –2.5% / +2.5% over temperature and over line and load regulation. Additionally, the LMZ10503 contains error nulling circuitry to substantially eliminate the feedback voltage variation over temperature as well as the long term aging effects of the internal amplifiers. In addition the zero nulling circuit dramatically reduces the 1/f noise of the bandgap amplifier and reference. The manifestation of this circuit action is that the duty cycle will have two slightly different but distinct operating points, each evident every other switching cycle.

#### 8.2.2.3 Loop Compensation

The LMZ10503 preserves flexibility by integrating the control components around the internal error amplifier while using three small external compensation components from V<sub>OUT</sub> to FB. An integrated type II (two pole, one zero) voltage-mode compensation network is featured. To ensure stability, an external resistor and small value capacitor can be added across the upper feedback resistor as a pole-zero pair to complete a type III (three pole, two zero) compensation network. The compensation components recommended in Table 4 provide type III compensation at an optimal control loop performance. The typical phase margin is 45° with a bandwidth of 80 kHz. Calculated output capacitance values not listed in Table 4 should be verified before designing into production. A detailed application note is available to provide verification support, AN-2013 (SNVA417). In general, calculated output capacitance values below the suggested value will have reduced phase margin and higher control loop bandwidth. Output capacitance values above the suggested values will experience a lower bandwidth and increased phase margin. Higher bandwidth is associated with faster system response to sudden changes such as load transients. Phase margin changes the characteristics of the response. Lower phase margin is associated with underdamped ringing and higher phase margin is associated with overdamped response. Losing all phase margin will cause the system to be unstable; an optimized area of operation is 30° to 60° of phase margin, with a bandwidth of 100 kHz ±20 kHz.

**LMZ10503**

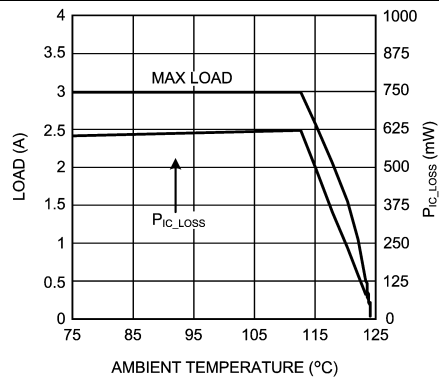
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[www.ti.com](http://www.ti.com)

**Figure 22. Loop Compensation Control Components**
**Table 4. LMZ10503 Compensation Component Values**

$V_{IN}$ (V)	$C_O$ ( $\mu$ F)	ESR (m $\Omega$ )		$R_{fbt}$ (k $\Omega$ ) <sup>(1)</sup>	$C_{comp}$ (pF) <sup>(1)</sup>	$R_{comp}$ (k $\Omega$ ) <sup>(1)</sup>
		MIN	MAX			
5	22	2	20	150	47	1
	47	2	20	100	100	4.53
	100	1	10	71.5	180	2
	150	1	5	56.2	270	0.499
	150	10	25	100	180	4.53
	150	26	50	182	100	8.25
	220	15	30	133	160	4.99
	220	31	60	200	100	6.98
3.3	22	2	20	100	56.2	5.62
	47	2	20	76.8	120	3.32
	100	1	10	49.9	220	1
	150	1	5	40.2	430	1
	150	10	25	43.2	390	3.32
	150	26	50	100	180	4.53
	220	15	30	80.6	240	3.32
	220	31	60	140	150	4.99

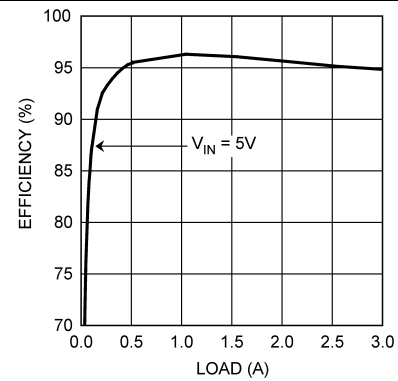
(1) In the special case where the output voltage is 0.8 V, TI recommends to remove  $R_{fbb}$  and keep  $R_{fbt}$ ,  $R_{comp}$ , and  $C_{comp}$  for a type III compensation.

## 8.2.3 Application Curves



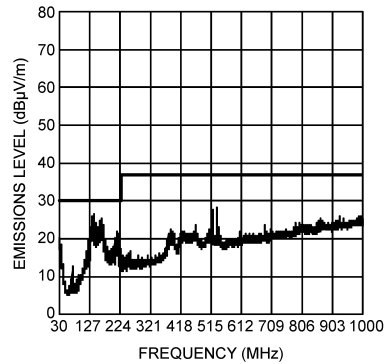
$V_{OUT} = 3.3\text{ V}$

**Figure 23. Current Derating**



$V_{OUT} = 3.3\text{ V}$

**Figure 24. Efficiency**

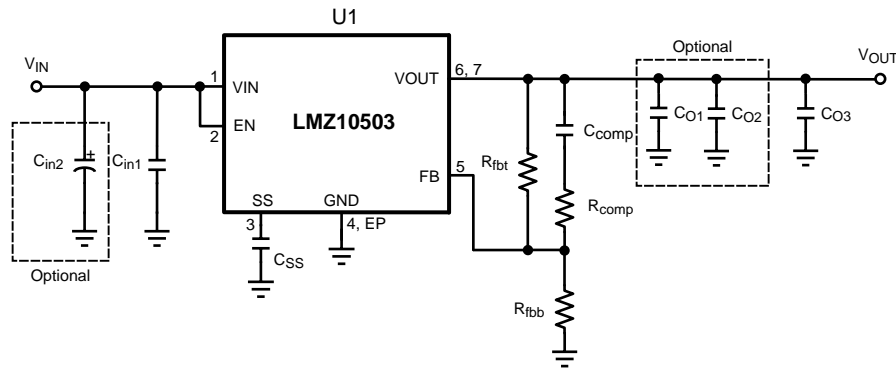


**Figure 25. Radiated Emissions (EN 55022, Class B)**

## 8.3 System Examples

### 8.3.1 Application Schematic for 3.3-V to 5-V Input and 2.5-V Output With Optimized Ripple and Transient Response

The compensation for each solution was optimized to work over the full input range. Many applications have a fixed input voltage rail. It is possible to modify the compensation to obtain a faster transient response for a given input voltage operating point.



**Figure 26. Optimized Schematic for 2.5-V Output Based on 3.3-V to 5-V Input**

**Table 5. Bill of Materials,  $V_{IN} = 3.3\text{ V}$  to  $5\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT (MAX)} = 3\text{ A}$ , Optimized for Low Input and Output Ripple Voltage and Fast Transient Response**

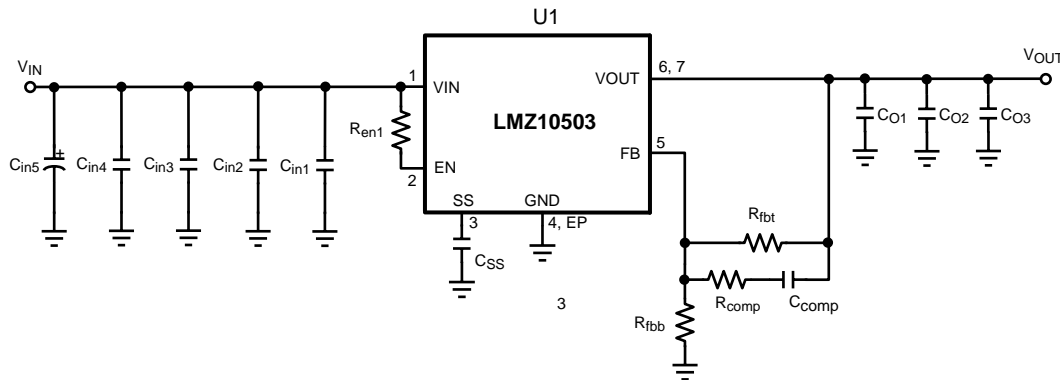
DESIGNATOR	DESCRIPTION	CASE SIZE	MANUFACTURER	MANUFACTURER P/N	QUANTITY
U1	SIMPLE SWITCHER	PFM-7	Texas Instruments	LMZ10503	1
$C_{in1}$	22 $\mu\text{F}$ , X5R, 10 V	1210	AVX	1210ZD226MAT	2
$C_{in2}$	220 $\mu\text{F}$ , 10 V, AL-Elec	E	Panasonic	EEE1AA221AP	1*
$C_{O1}$	4.7 $\mu\text{F}$ , X5R, 10 V	0805	AVX	0805ZD475MAT	1*
$C_{O2}$	22 $\mu\text{F}$ , X5R, 6.3 V	1206	AVX	12066D226MAT	1*
$C_{O3}$	100 $\mu\text{F}$ , X5R, 6.3 V	1812	AVX	18126D107MAT	1
$R_{fbt}$	75 k $\Omega$	0402	Vishay Dale	CRCW040275K0FKED	1
$R_{fbb}$	34.8 k $\Omega$	0402	Vishay Dale	CRCW040234K8FKED	1
$R_{comp}$	1.0 k $\Omega$	0402	Vishay Dale	CRCW04021K00FKED	1
$C_{comp}$	220 pF, $\pm 5\%$ , C0G, 50 V	0402	Murata	GRM1555C1H221JA01D	1
$C_{SS}$	10 nF, $\pm 10\%$ , X7R, 16 V	0402	Murata	GRM155R71C103KA01	1

**Table 6. Output Voltage Setting ( $R_{fbt} = 75\text{ k}\Omega$ )**

$V_{OUT}$	$R_{fbb}$
3.3V	23.7 k $\Omega$
2.5 V	34.8 k $\Omega$
1.8 V	59 k $\Omega$
1.5 V	84.5 k $\Omega$
1.2 V	150 k $\Omega$
0.9 V	590 k $\Omega$

### 8.3.2 Application Schematic for 3.3-V to 5-V Input and 2.5-V Output

The compensation for each solution was optimized to work over the full input range. Many applications have a fixed input voltage rail. It is possible to modify the compensation to obtain a faster transient response for a given input voltage operating point.



**Figure 27. Schematic for 2.5-V Output Based on 3.3-V to 5-V Input**

**Table 7. Bill of Materials for Evaluation Board,  $V_{IN} = 3.3\text{ V to }5\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT (MAX)} = 3\text{ A}$**

DESIGNATOR	DESCRIPTION	CASE SIZE	MANUFACTURER	MANUFACTURER P/N	QUANTITY
U1	SIMPLE SWITCHER	PFM-7	Texas Instruments	LMZ10503	1
C <sub>in1</sub>	1 $\mu\text{F}$ , X7R, 16 V	0805	TDK	C2012X7R1C105K	1
C <sub>in2</sub> , C <sub>O1</sub>	4.7 $\mu\text{F}$ , X5R, 6.3 V	0805	TDK	C2012X5R0J475K	2
C <sub>in3</sub> , C <sub>O2</sub>	22 $\mu\text{F}$ , X5R, 16 V	1210	TDK	C3225X5R1C226M	2
C <sub>in4</sub>	47 $\mu\text{F}$ , X5R, 6.3 V	1210	TDK	C3225X5R0J476M	1
C <sub>in5</sub>	220 $\mu\text{F}$ , 10 V, AL-Elec	E	Panasonic	EEE1AA221AP	1
C <sub>O3</sub>	100 $\mu\text{F}$ , X5R, 6.3 V	1812	TDK	C4532X5R0J107M	1
R <sub>fbt</sub>	75 k $\Omega$	0805	Vishay Dale	CRCW080575K0FKEA	1
R <sub>fbb</sub>	34.8 k $\Omega$	0805	Vishay Dale	CRCW080534K8FKEA	1
R <sub>comp</sub>	1.1 k $\Omega$	0805	Vishay Dale	CRCW08051K10FKEA	1
C <sub>comp</sub>	180 pF, $\pm 5\%$ , C0G, 50 V	0603	TDK	C1608C0G1H181J	1
R <sub>en1</sub>	100 k $\Omega$	0805	Vishay Dale	CRCW0805100KFKEA	1
C <sub>SS</sub>	10 nF, $\pm 5\%$ , C0G, 50 V	0805	TDK	C2012C0G1H103J	1

**Table 8. Output Voltage Setting ( $R_{fbt} = 75\text{ k}\Omega$ )**

$V_{OUT}$	$R_{fbb}$
3.3V	23.7 k $\Omega$
2.5 V	34.8 k $\Omega$
1.8 V	59 k $\Omega$
1.5 V	84.5 k $\Omega$
1.2 V	150 k $\Omega$
0.9 V	590 k $\Omega$

## LMZ10503

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### 8.3.3 EMI Tested Schematic for 2.5-V Output Based on 3.3-V to 5-V Input

The compensation for each solution was optimized to work over the full input range. Many applications have a fixed input voltage rail. It is possible to modify the compensation to obtain a faster transient response for a given input voltage operating point.

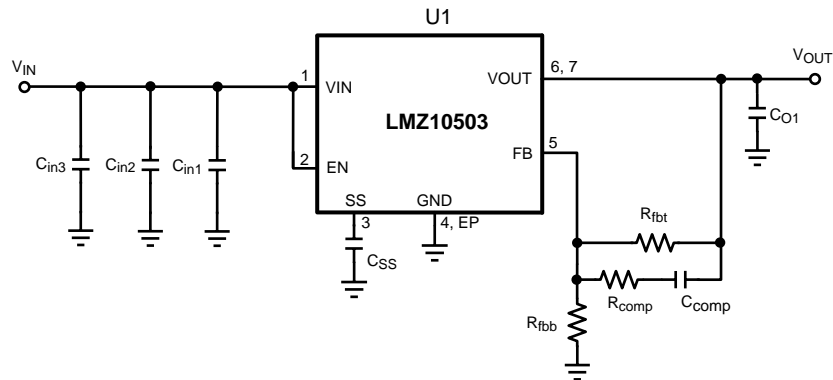


Figure 28. EMI Tested Schematic for 2.5-V Output Based on 3.3-V to 5-V Input

Table 9. Bill of Materials,  $V_{IN} = 5\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT (MAX)} = 3\text{ A}$ , Tested With EN55022 Class B Radiated Emissions

DESIGNATOR	DESCRIPTION	CASE SIZE	MANUFACTURER	MANUFACTURER P/N	QUANTITY
U1	SIMPLE SWITCHER	PFM-7	Texas Instruments	LMZ10503	1
$C_{in1}$	1 $\mu\text{F}$ , X7R, 16 V	0805	TDK	C2012X7R1C105K	1
$C_{in2}$	4.7 $\mu\text{F}$ , X5R, 6.3 V	0805	TDK	C2012X5R0J475K	1
$C_{in3}$	47 $\mu\text{F}$ , X5R, 6.3 V	1210	TDK	C3225X5R0J476M	1
$C_{O1}$	100 $\mu\text{F}$ , X5R, 6.3 V	1812	TDK	C4532X5R0J107M	1
$R_{fbt}$	75 k $\Omega$	0805	Vishay Dale	CRCW080575K0FKEA	1
$R_{fbb}$	34.8 k $\Omega$	0805	Vishay Dale	CRCW080534K8FKEA	1
$R_{comp}$	1.1 k $\Omega$	0805	Vishay Dale	CRCW08051K10FKEA	1
$C_{comp}$	180 pF, $\pm 5\%$ , C0G, 50 V	0603	TDK	C1608C0G1H181J	1
$C_{SS}$	10 nF, $\pm 5\%$ , C0G, 50 V	0805	TDK	C2012C0G1H103J	1

Table 10. Output Voltage Setting ( $R_{fbt} = 75\text{ k}\Omega$ )

$V_{OUT}$	$R_{fbb}$
3.3 V	23.7 k $\Omega$
2.5 V	34.8 k $\Omega$
1.8 V	59 k $\Omega$
1.5 V	84.5 k $\Omega$
1.2 V	150 k $\Omega$
0.9 V	590 k $\Omega$

## 9 Power Supply Recommendations

The LMZ10503 device is designed to operate from an input voltage supply range between 2.95 V and 5.5 V. This input supply should be well regulated and able to withstand maximum input current and maintain a stable voltage. The resistance of the input supply rail should be low enough that an input current transient does not cause a high enough drop at the LMZ10503 supply voltage that can cause a false UVLO fault triggering and system reset. If the input supply is more than a few inches from the LMZ10503, additional bulk capacitance may be required in addition to the ceramic bypass capacitors. The amount of bulk capacitance is not critical, but a 47- $\mu$ F or 100- $\mu$ F electrolytic capacitor is a typical choice.

## 10 Layout

### 10.1 Layout Guidelines

The PCB copper heat sink must be connected to the exposed pad (EP). Approximately thirty six, 8 mil thermal vias spaced 59 mils (1.5 mm) apart must connect the top copper to the bottom copper. For an extended discussion and formulations of thermal rules of thumb, refer to AN-2020 ([SNVA419](#)). For an example of a high thermal performance PCB layout with  $\theta_{JA}$  of 20°C/W, refer to the evaluation board application note AN-2022 ([SNVA421](#)) and for results of a study of the effects of the PCB designs, refer to AN-2026 ([SNVA424](#)).

PCB layout is an important part of DC-DC converter design. Poor board layout can disrupt the performance of a DC-DC converter and surrounding circuitry by contributing to EMI, ground bounce and resistive voltage drop in the traces. These can send erroneous signals to the DC-DC converter resulting in poor regulation or instability. Good layout can be implemented by following a few simple design rules.

- 1. Minimize area of switched current loops.**

From an EMI reduction standpoint, it is imperative to minimize the high di/dt current paths. The high current that does not overlap contains high di/dt, see [Figure 29](#). Therefore physically place input capacitor ( $C_{in1}$ ) as close as possible to the LMZ10503 VIN pin and GND exposed pad to avoid observable high-frequency noise on the output pin. This will minimize the high di/dt area and reduce radiated EMI. Additionally, grounding for both the input and output capacitor should consist of a localized top side plane that connects to the GND exposed pad (EP).

- 2. Have a single point ground.**

The ground connections for the feedback, soft-start, and enable components should be routed only to the GND pin of the device. This prevents any switched or load currents from flowing in the analog ground traces. If not properly placed, poor grounding can result in degraded load regulation or erratic output voltage ripple behavior. Provide the single point ground connection from pin 4 to EP.

- 3. Minimize trace length to the FB pin.**

Both feedback resistors,  $R_{fbt}$  and  $R_{fbb}$ , and the compensation components,  $R_{comp}$  and  $C_{comp}$ , should be located close to the FB pin. Since the FB node is high impedance, keep the copper area as small as possible. This is most important as relatively high value resistors are used to set the output voltage.

- 4. Make input and output bus connections as wide as possible.**

This reduces any voltage drops on the input or output of the converter and maximizes efficiency. To optimize voltage accuracy at the load, ensure that a separate feedback voltage sense trace is made at the load. Doing so will correct for voltage drops and provide optimum output accuracy.

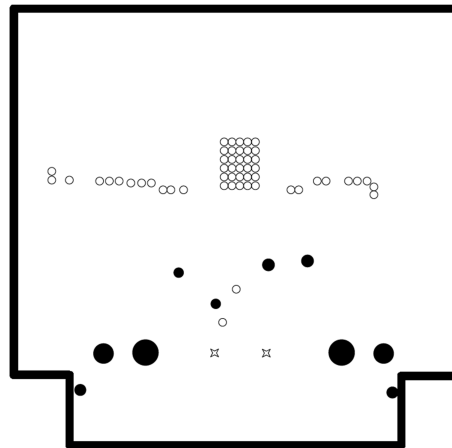
- 5. Provide adequate device heat-sinking.**

Use an array of heat-sinking vias to connect the exposed pad to the ground plane on the bottom PCB layer. If the PCB has multiple copper layers, thermal vias can also be employed to make connection to inner layer heat-spreading ground planes. For best results use a 6 × 6 via array with minimum via diameter of 8 mils thermal vias spaced 59 mils (1.5 mm). Ensure enough copper area is used for heat-sinking to keep the junction temperature below 125°C.

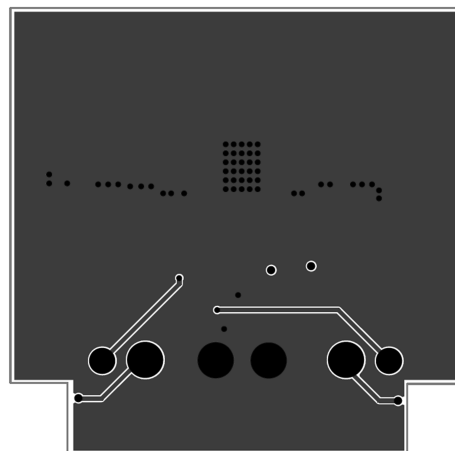




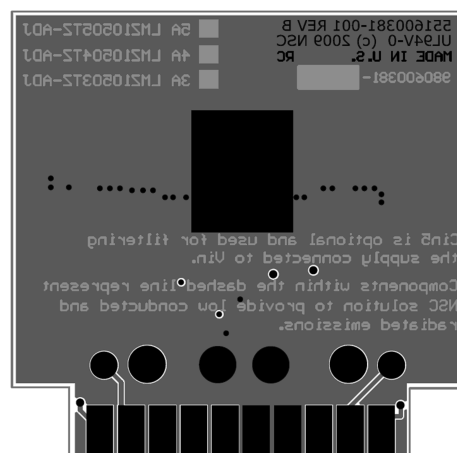
## Layout Examples (continued)



**Figure 32. Internal Layer 1 (Ground)**



**Figure 33. Internal Layer 2 (Ground and Signal Traces)**



**Figure 34. Bottom Copper**

### 10.3 Estimate Power Dissipation and Thermal Considerations

Use the current derating curves in the [Typical Characteristics](#) section to obtain an estimate of power loss ( $P_{IC\_LOSS}$ ). For the design case of  $V_{IN} = 5\text{ V}$ ,  $V_{OUT} = 2.5\text{ V}$ ,  $I_{OUT} = 3\text{ A}$ ,  $T_{A(MAX)} = 85^\circ\text{C}$ , and  $T_{J(MAX)} = 125^\circ\text{C}$ , the device must see a thermal resistance from case to ambient ( $\theta_{CA}$ ) of less than:

$$\theta_{CA} \geq \frac{T_{J(MAX)} - T_{A(MAX)}}{P_{IC\_LOSS}} - \theta_{JC} \quad (21)$$

$$\theta_{CA} < \frac{125^\circ\text{C} - 85^\circ\text{C}}{0.56\text{ W}} - 1.9 \frac{^\circ\text{C}}{\text{W}} < 69.5 \frac{^\circ\text{C}}{\text{W}} \quad (22)$$

Given the typical thermal resistance from junction to case ( $\theta_{JC}$ ) to be  $1.9^\circ\text{C/W}$  (typical). Continuously operating at a  $T_J$  greater than  $125^\circ\text{C}$  will have a shorten life span.

To reach  $\theta_{CA} = 69.5^\circ\text{C/W}$ , the PCB is required to dissipate heat effectively. With no airflow and no external heat, a good estimate of the required board area covered by 1-oz. copper on both the top and bottom metal layers is:

$$\text{Board Area}_{cm^2} \geq \frac{500}{\theta_{CA}} \cdot \frac{^\circ\text{C} \times cm^2}{W} \quad (23)$$

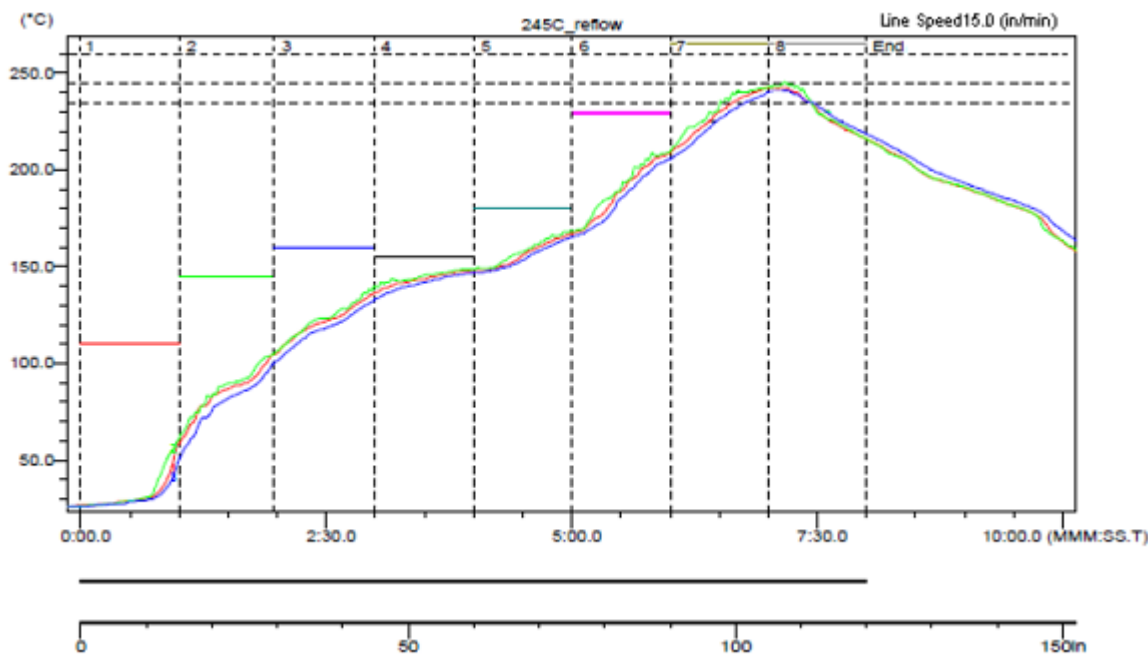
$$\text{Board Area}_{cm^2} \geq \frac{500}{69.5 \frac{^\circ\text{C}}{W}} \cdot \frac{^\circ\text{C} \times cm^2}{W} \quad (24)$$

As a result, approximately 7.2 square cm of 1-oz. copper on top and bottom layers is required for the PCB design.

## 10.4 Power Module SMT Guidelines

The recommendations below are for a standard module surface mount assembly

- Land Pattern – Follow the PCB land pattern with either soldermask defined or non-soldermask defined pads
- Stencil Aperture
  - For the exposed die attach pad (DAP), adjust the stencil for approximately 80% coverage of the PCB land pattern
  - For all other I/O pads use a 1:1 ratio between the aperture and the land pattern recommendation
- Solder Paste – Use a standard SAC Alloy such as SAC 305, type 3 or higher
- Stencil Thickness – 0.125 to 0.15 mm
- Reflow - Refer to solder paste supplier recommendation and optimized per board size and density
- Maximum number of reflows allowed is one
- Refer to AN *Design Summary LMZ1xxx and LMZ2xxx Power Modules Family* ([SNAA214](#)) for reflow information.



**Figure 35. Sample Reflow Profile**

**Table 11. Sample Reflow Profile Table**

PROBE	MAX TEMP (°C)	REACHED MAX TEMP	TIME ABOVE 235°C	REACHED 235°C	TIME ABOVE 245°C	REACHED 245°C	TIME ABOVE 260°C	REACHED 260°C
1	242.5	6.58	0.49	6.39	0.00	–	0.00	–
2	242.5	7.10	0.55	6.31	0.00	7.10	0.00	–
3	241.0	7.09	0.42	6.44	0.00	–	0.00	–

## 11 Device and Documentation Support

### 11.1 Device Support

#### 11.1.1 Third-Party Products Disclaimer

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#### 11.1.2 Development Support

For developmental support, see the following:

WEBENCH Tool, <http://www.ti.com/webench>

### 11.2 Documentation Support

#### 11.2.1 Related Documentation

For related documentation, see the following:

- AN-2027 *Inverting Application for the LMZ14203 SIMPLE SWITCHER Power Module*, [SNVA425](#))
- *Absolute Maximum Ratings for Soldering*, [SNOA549](#))
- AN-2024 *LMZ1420x / LMZ1200x Evaluation Board* ([SNVA422](#))
- AN-2020 *Thermal Design By Insight, Not Hindsight* ([SNVA419](#))
- AN-2026 *Effect of PCB Design on Thermal Performance of SIMPLE SWITCHER Power Modules* ([SNVA424](#))
- *Design Summary LMZ1xxx and LMZ2xxx Power Modules Family* ([SNAA214](#))

### 11.3 Community Resources

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### 11.5 Electrostatic Discharge Caution



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

### 11.6 Glossary

[SLYZ022](#) — *TI Glossary*.

This glossary lists and explains terms, acronyms, and definitions.

## 12 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

## PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
LMZ10503TZ-ADJ/NOPB	ACTIVE	TO-PMOD	NDW	7	250	Green (RoHS & no Sb/Br)	CU SN	Level-3-245C-168 HR	-40 to 85	LMZ10503 TZ-ADJ	<a href="#">Samples</a>
LMZ10503TZE-ADJ/NOPB	ACTIVE	TO-PMOD	NDW	7	45	Green (RoHS & no Sb/Br)	CU SN	Level-3-245C-168 HR	-40 to 85	LMZ10503 TZ-ADJ	<a href="#">Samples</a>
LMZ10503TZX-ADJ/NOPB	ACTIVE	TO-PMOD	NDW	7	500	Green (RoHS & no Sb/Br)	CU SN	Level-3-245C-168 HR	-40 to 85	LMZ10503 TZ-ADJ	<a href="#">Samples</a>

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBSOLETE:** TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

**TBD:** The Pb-Free/Green conversion plan has not been defined.

**Pb-Free (RoHS):** TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

**Pb-Free (RoHS Exempt):** This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

**Green (RoHS & no Sb/Br):** TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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**TAPE AND REEL INFORMATION**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LMZ10503TZ-ADJ/NOPB	TO-PMOD	NDW	7	250	330.0	24.4	10.6	14.22	5.0	16.0	24.0	Q2
LMZ10503TZ-ADJ/NOPB	TO-PMOD	NDW	7	500	330.0	24.4	10.6	14.22	5.0	16.0	24.0	Q2



## TAPE AND REEL BOX DIMENSIONS



\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LMZ10503TZ-ADJ/NOPB	TO-PMOD	NDW	7	250	367.0	367.0	45.0
LMZ10503TZ-ADJ/NOPB	TO-PMOD	NDW	7	500	367.0	367.0	45.0



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