

Efficient Implementation of Mamba Architecture for Radio-based Localisation Using LuViRA datasets

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Abstract—This paper investigates three Mamba-based models variant on the LuViRA [1] dataset and demonstrates the effectiveness of SSM-based architectures for indoor radio localization. Building on these findings, we propose task-oriented simplifications that preserve comparable inference accuracy while significantly reducing model size, hardware cost, and end-to-end training/inference overhead. To further enable deployment, we implement a synthesizable FPGA accelerator for the state-space model (SSM) hotspot in Mamba, targeting indoor radio localization (LuViRA). Software profiling identifies the SSM forward path as a dominant runtime contributor. We implement SSM as a streaming pipeline using three primitives (MAC, EWA, EWM) and a LUT-based sigmoid, with a $4 \times 4 \times 4$ pipelined MVM array, interleaving memory access, and FIFO-based AXI-Stream control for backpressure-safe composition. The integrated module closes timing at 400 MHz using 76 DSPs and 6,244 LUTs, with an estimated on-chip power of 1.442 W, providing a baseline toward end-to-end Mamba inference.

Keywords—Mamba, state-space model (SSM), indoor localization, massive MIMO, FPGA acceleration.

I. INTRODUCTION

INDOOR radio localization requires modeling high-dimensional wireless signals with strong temporal dynamics and multipath effects. As antenna/channel dimensions increase, conventional FCNN-based regressors become inefficient: their parameter count and compute cost grow rapidly with input width, making deployment and scaling difficult [2]. This motivates architectures that can process long signal sequences with stronger parameter efficiency.

Mamba, as a modern state-space-model (SSM) architecture, offers a compelling alternative. Instead of relying on dense fully connected mappings over the full input history, Mamba uses recurrent state updates to summarize historical information compactly, enabling effective memory of temporal context with linear-time sequence processing. Its SSM-style recursive computation is naturally aligned with long-sequence modeling, where maintaining and updating latent states is more efficient than repeatedly recomputing global interactions. For indoor localization, this is particularly attractive: the model can capture temporal patterns induced by motion and multipath evolution while avoiding the parameter explosion common in FCNNs under increasing channel dimensions. Therefore, Mamba provides a practical path toward accurate, scalable, and hardware-friendly radio localization systems.

In this project, we follow a software-to-hardware co-design path on the LuViRA dataset [1] and evaluate three Mamba-family variants for radio localization. We first adopted a Channel-Mamba-style design to support multi-domain feature fusion (e.g., CIR real/imag, power, and optional differential features), motivated by potential cross-channel interaction

and extensibility to future multi-modal inputs (e.g., audio). However, experiments show that, under the current setting, additional channel-fusion branches bring only limited accuracy gain (typically around 3–4%) while introducing substantial overhead in model complexity, training time, and hardware mapping cost.

Based on this observation, we revisited vanilla Mamba and analyzed the temporal context length for the target workload. We found that a short window ($K = 16$) yields the best trade-off, indicating that very strong long-range state modeling is not always necessary for this short-horizon localization task and may introduce redundancy. We therefore proposed a hardware-friendly simplification of Mamba v1 that preserves comparable inference accuracy while reducing model size and end-to-end runtime overhead.

From a deployment perspective, acceleration should target real runtime hotspots. Profiling (Table I) shows that the SSM forward path dominates execution, so we implement it with a fully synthesizable FPGA design. The accelerator uses a streaming pipeline built from MAC, EWA, and EWM operators plus a LUT-based sigmoid, and scales via a $4 \times 4 \times 4$ pipelined MVM array, interleaving memory access, and FIFO-based AXI-Stream flow control for backpressure-safe composition.

Although recent studies have explored Mamba acceleration from complementary angles, including hardware-algorithm co-design [3], reconfigurable operator support [4], and hybrid dataflows [5], several trade-offs remain under-discussed for radio-localization-oriented FPGA deployment. First, compute-array organization is often fixed without controlled comparison under identical workload assumptions. Second, memory organization for mixed linear and element-wise SSM pipelines is not sufficiently analyzed, especially for interleaved banked access. Third, control granularity trade-offs between coarse scheduling and fine-grained streaming are rarely quantified under the same constraints.

Motivated by these gaps, this work contributes: 1) an empirical software-side study from Channel Mamba to simplified Mamba for short-window localization, 2) a hotspot-driven FPGA mapping of the SSM datapath, and 3) a consistent evaluation of array, memory, and control trade-offs. The rest of this report first presents SSM decomposition and hardware mapping, then details the accelerator architecture and implementation results.

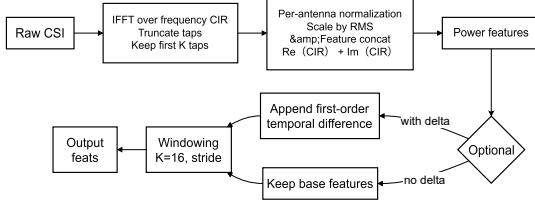


Fig. 1. Data preprocessing pipeline from CSI to model-ready features.

TABLE I
FUNCTION PROFILING SUMMARY.

Function	Time	Share
_PointWise1X1.forward	30	7.75
_QuantConv1d.forward	57	14.73
RMSNorm.forward	140	36.18
SelectiveScanIC.forward	160	41.34
Total (listed)	387	100.00

II. SOFTWARE EXPLORATION AND TASK-DRIVEN SIMPLIFICATION

This section presents the software-side exploration that guided our final model choice and hardware-oriented redesign. We start from a Channel-Mamba-style architecture for multi-domain feature fusion, then progressively simplify the model based on empirical evidence under the LuViRA workload.

A. Task Setting and Data Pipeline

We target indoor localization on LuViRA, where each recording is a time–frequency–space CSI tensor ($T \approx 4000$ at 100 Hz, 100 antennas, 100 subcarriers). To align software processing with deployment-oriented constraints, we organize the dataflow in a hardware-friendly manner with sequential window access and compact per-frame storage.

Raw CSI is converted into model-ready features through: (1) IFFT-based CIR extraction over subcarriers, (2) tap truncation, and (3) feature construction using CIR real/imaginary components, per-antenna log-power, and optional first-order temporal difference. For each trajectory/grid file, we store `base.feats.npy`, `base.xy.npy`, and `base.ts.npy`, while `base.json` records role-aware window indices (train/eval/test), window length, stride, and feature configuration. This layout supports on-demand window generation without offline materialization of all training samples.

In our final experiments, we enable `--preload`, which significantly improves training throughput by avoiding repeated data fetch/transfer overhead across iterations. At the same time, the pipeline still supports lazy-loading mode for resource-constrained platforms, and we verified stable operation on a low-end MX330 GPU setup. Although preload increases memory usage, the overhead remains acceptable for our workload (GPU memory usage rises from approximately 0.3 GB to 1.4 GB), while the training speedup is substantial. Finally, we compute train-only global normalization statistics (`stats_train.npz`, mean/std with std-floor) to ensure stable scaling across grids and avoid evaluation/test leakage.

B. Initial Design: Channel Mamba for Multi-domain Fusion

Our initial hypothesis was that Channel Mamba could better exploit heterogeneous input domains (e.g., CIR, power, and differential signals), while also providing a natural extension path to future multi-modal inputs such as audio. Accordingly, we first implemented a multi-branch Channel-Mamba-style model with explicit channel fusion blocks.

C. Empirical Reassessment

Despite the above motivation, experiments show that the additional fusion complexity yields only limited accuracy gains in the current setting (typically around 3–4%), while significantly increasing parameter count, training cost, and hardware mapping overhead due to extra branches and block-level computation. In particular, differential features bring marginal improvement, which does not justify the induced structural complexity for deployment-oriented design.

D. Task-driven Simplification of Mamba

We then revisited vanilla Mamba and conducted multi-round comparisons across window lengths and architectural variants. A consistent observation is that $K = 16$ provides the best trade-off for this task. This indicates a short-horizon localization regime where overly strong long-range memory can be redundant and may even hurt generalization. Based on this, we simplified Mamba v1 into a hardware-friendly form by removing non-essential complexity while preserving the key selective recurrent behavior required by the task.

E. Final Model and Key Differences

Compared with the original Mamba, the final model keeps the core recurrent update path but adopts a more regular and deployment-friendly structure (fewer branches, reduced state/update complexity, and more hardware-compatible operators). This redesign preserves comparable localization accuracy while reducing model size and improving training/inference efficiency, making it better aligned with FPGA implementation constraints.

III. SSM DECOMPOSITION AND HARDWARE MAPPING

From an algorithmic perspective, the SSM core can be decomposed into three major steps: (1) *dt_projection*, which derives step-size coefficients Δ_t from the current input; (2) *state update*, the time-recursive selective scan (recurrent update) that fuses the current input with the previous state to produce a new state s_t ; and (3) *output gate*, which combines the updated state with the gating branch to form the output. This decomposition is consistent with Fig. 2, where the input is split into a main branch and a gate branch after the `in_proj` layer; the main branch is locally modulated and then fed into the SSM for state update, while the output is produced via element-wise interaction with the gate.

When mapped to hardware, the SSM can be reduced to three key hardware primitives:

- **MAC** (matrix–vector multiply–accumulate) for *dt_proj*.

$$\lambda_t = \sigma(W\Delta u_t + b) \quad (1)$$

TABLE II
COMPARISON OF MODEL VARIANTS ON LUViRA (TO BE FILLED WITH YOUR MEASURED RESULTS).

Model	Input Features	Params	Train Time / epoch (s)	iterations per second (it/s)	EPE Mean (cm)	HW Cost	Proxy
FCNN	CIR	440 MB	N/A	N/A	13	HIGH	
Channel Mamba	CIR + Power	40.4 MB	73	13.18	12.9	High	
Vanilla Mamba v1	CIR + Power	3.38 MB	33	32.62	24.7	Medium	
Simplified Mamba	CIR + Power	3.40 MB	13	75.30	13.5	Low	

TABLE III
MODULE-LEVEL DIFFERENCES BETWEEN ORIGINAL MAMBA AND THE PROPOSED SIMPLIFIED VARIANT.

Component	Original Mamba	Simplified Mamba (Ours)	Impact
Input fusion path	Multi-branch / channel-fusion-friendly design with extra structural overhead.	Reduced branches and regularized single-path backbone.	Lower control complexity and easier hardware scheduling.
State update (SSM)	Full selective scan parameterization with higher arithmetic and control complexity.	Hardware-friendly selective recurrence with reduced state-update complexity.	Faster execution and easier FPGA mapping.
Temporal context usage	Strong long-range modeling capacity designed for longer contexts.	Tuned for short-window localization ($K < 16$).	Better task fit; less redundancy and lower overfitting risk.
Operator pattern	Mixed operators with heavier scheduling burden.	More regular Conv/element-wise-friendly computation flow.	Better pipelining and implementation regularity.
Model size / compute	Higher parameter and compute cost.	Lower parameter and compute cost.	Reduced memory footprint and MAC demand.

TABLE IV
ABLATION ON WINDOW LENGTH K WITH PATCH LENGTH/STRIDE VARIANTS (LUViRA).

K (pl, s)	Eval mean err (m)	Test mean err (m)
1 (1,1)	0.10068	0.135
2 (2,2)	0.09557	0.135
4 (2,2)	0.09814	0.139
8 (2,2)	0.09405	0.141
4 (4,4)	0.09983	0.137
6 (4,4)	0.09839	0.138
8 (4,4)	0.09749	0.144
8 (8,4)	0.09744	0.152
12 (8,4)	0.09286	0.156
16 (8,4)	0.09225	0.161
24 (8,4)	0.09432	0.159
32 (8,4)	0.09328	0.166

- **EWA** (element-wise add) for state update.

$$s_t = \lambda_t \odot s_{t-1} + (1 - \lambda_t) \odot u_t \quad (2)$$

- **EWM** (element-wise multiply) for output gating.

$$y_t = s_t \odot g_t \quad (3)$$

Therefore, our design builds a streaming accelerator using **MVM (MAC)** + **EWA** + **EWM** as the core building blocks, centered on the SSM state-update hotspot.

Fig. 3 illustrates the top-level data path of our accelerator, which can be summarized into four stages. (i) **Linear compute and reduction**: the input vector is streamed from `xt_buf`, weights are supplied by `WBUF`, and a $4 \times 4 \times 4$ MAC array produces partial sums that are reduced by a reduction tree, forming the linear-layer outputs. (ii) **Nonlinearity and gate preparation**: the linear outputs are bias-adjusted, decoupled by a FIFO, and passed through a Sigmoid LUT to generate gate-related coefficients, aligning with the gate path. (iii) **State update (Element-wise update + s_buffer)**: a `Join` module

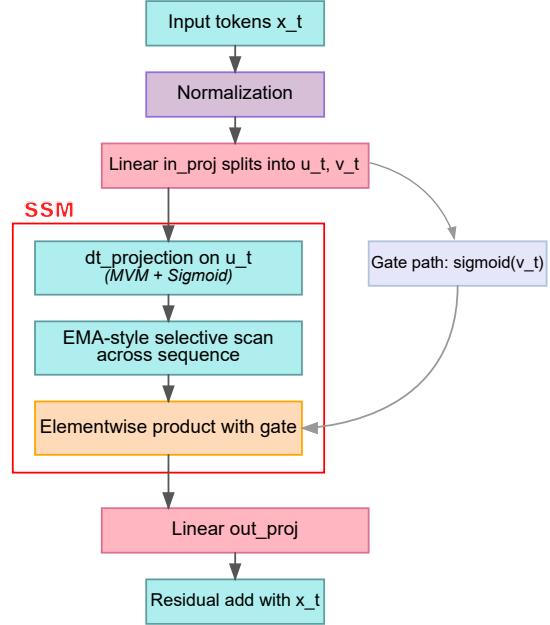


Fig. 2. Algorithmic view of the Mamba block [6].

aligns the required streams (e.g., λ and x_t) and feeds the element-wise update unit that performs combined **EWM/EWA** operations to produce s_{new} , with `s_buffer` closing the read-old/write-new loop for recurrent state updates. (iv) **Output gate**: the updated state and the gate stream are aligned by another `Join`, decoupled by a FIFO, and multiplied element-wise in the EWM gate to produce y_{out} .

This organization keeps the SSM workload concentrated on the **MAC array (MVM)** and **element-wise (EWA/EWM)** modules, while FIFO and AXI-streaming boundaries enable fine-grained pipelining and robust backpressure propagation.

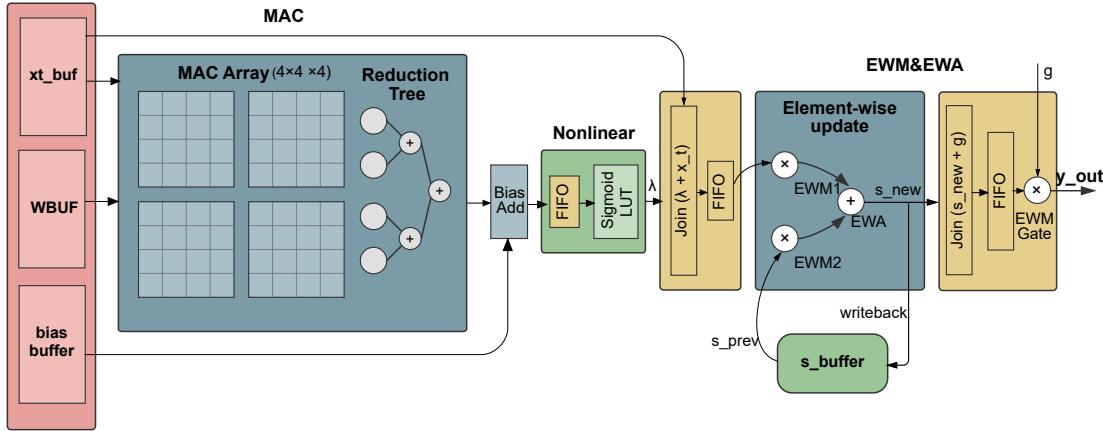


Fig. 3. Top-level architecture of the proposed accelerator (based on the Mamba/SSM operator structure) [6].

IV. METHOD

A. MAC Array Design and Architecture Selection

This chapter presents the hardware implementation methods of our SSM accelerator, starting from the compute backbone: the MAC array. For the SSM datapath, linear layers dominate the arithmetic cost and can be reduced to an MVM of size $(256 \times 256) \cdot (256 \times 1)$, i.e., $256 \times 256 = 65,536$ MAC operations. A useful throughput bound is

$$CC_{\min} = \left\lceil \frac{\text{Total MAC operations}}{\#\text{PEs}} \right\rceil, \quad (4)$$

which makes explicit the fundamental trade-off between parallelism (DSP/PE count) and latency in cycles.

We compare three candidate array organizations.

1)

2) A 16×16 systolic array offers strong spatial reuse for GEMM (both operands reuse across the 2D array) and can theoretically complete a tile in 256 cycles. For GEMV, weights have little spatial reuse (each $W_{i,k}$ is typically consumed once per input), making the design weight-bandwidth dominated: full utilization would require streaming ~ 256 weights/cycle, which also increases routing pressure and complicates timing closure in practice.

3) A 64×1 single-column GEMV engine directly addresses the bandwidth bottleneck and is well matched to GEMV-style computation, achieving a 1024-cycle latency under a 64 weights/cycle budget. However, a full Mamba pipeline also includes matrix-matrix operations beyond the SSM core (e.g., input and output linear projection), so a one-column GEMV structure is less reusable for those kernels and is therefore suboptimal for long-term extensibility.

4) Our proposed $4 \times 4 \times 4$ pipelined MAC array is a compromise: it preserves the 64 weights/cycle bandwidth target and achieves a similar 1024-cycle-class latency as the 64×1 baseline, while improving routing scalability relative to a monolithic systolic array and enabling higher reuse across multiple kernels.

The compute engine instantiates four parallel 4×4 MAC sub-arrays (ARRAY1–ARRAY4), forming a $4 \times 4 \times 4$ pipeline

organization. Each 4×4 sub-array consumes a 4-element slice of the input vector x_t together with a 4×4 weight block per cycle. Each array performs a local 4×4 MVM and accumulates the partial sums from the last cycle. After 4 cycles, all four sub-arrays have been used and the pipeline is fully filled. Importantly, the sub-array does **not** directly output four independent column-wise partial sums. Instead, it maintains accumulation across the tile and produces an **already-accumulated 4×4 partial-result matrix** at its output interface. This 4×4 partial-result matrix is then forwarded to a dedicated **three-level reduction tree**, which hierarchically reduces the 4×4 block into the required vector-form output used by subsequent stages.

With this organization, the MAC fabric focuses on dense local accumulation, while the reduction tree provides a structured and timing-friendly path to obtain the final MVM vector output. After a short fill phase, all four sub-arrays run concurrently in steady state, hiding control overhead while keeping the compute fabric small (64 MACs total), which is favorable for FPGA timing closure. Table V provides the full weight-column schedule;

TABLE VI
COLUMN START PROGRESSION PER SUB-ARRAY.

Array	Column Start Points	Δ
Array1	$0 \rightarrow 16 \rightarrow 32 \rightarrow 48 \rightarrow 64$	+16
Array2	$4 \rightarrow 20 \rightarrow 36 \rightarrow 52$	+16
Array3	$8 \rightarrow 24 \rightarrow 40$	+16
Array4	$12 \rightarrow 28$	+16

TABLE VII
CONSTANT 12-COLUMN SPACING BETWEEN ADJACENT ARRAYS WITHIN THE SAME CYCLE.

Cycle	$A1 \rightarrow A2 \Delta$	$A2 \rightarrow A3 \Delta$	$A3 \rightarrow A4 \Delta$
2	$16-4 = 12$	—	—
3	$32-20 = 12$	$20-8 = 12$	—
4	$48-36 = 12$	$36-24 = 12$	$24-12 = 12$
5	$64-52 = 12$	$52-40 = 12$	$40-28 = 12$

Weights are scheduled in 4-column blocks. For each sub-array, the column start index advances by a fixed stride of +16 every cycle. Within the same cycle, the four sub-arrays access distinct column blocks with fixed offsets $\{0, 4, 8, 12\}$,

TABLE V
WEIGHT INPUT COLUMN SCHEDULING FOR THE $4 \times 4 \times 4$ PIPELINED MAC ARRAY.

Cycle	Array1 Columns	Array2 Columns	Array3 Columns	Array4 Columns	Description
1	col0–3	–	–	–	ARRAY1 preloads first 4×4 block (tile1).
2	col16–19	col4–7	–	–	ARRAY2 begins tile1.
3	col32–35	col20–23	col8–11	–	ARRAY3 begins tile1 (3-cycle stagger).
4	col48–51	col36–39	col24–27	col12–15	ARRAY4 joins; pipeline full.
5–16	continue +16 stride	same	same	same	Steady-state loading of tile1.
17	col256–259 → tile2	col244–247	col232–235	col220–223	ARRAY1 starts tile2 (row4–7).
18	col272–275	col260–263 → tile2	col248–251	col236–239	ARRAY2 switches to tile2.
19	col288–291	col276–279	col264–267 → tile2	col252–255	ARRAY3 switches to tile2.
20	col304–307	col292–295	col280–283	col268–271 → tile2	ARRAY4 switches; tile1 finishes.
21–37	continue +16 stride	same	same	same	Steady-state operation for tile2.
38	tile3 preload	–	–	–	ARRAY1 starts tile3.
39	–	tile3 preload	–	–	ARRAY2 starts tile3.
40	–	–	tile3 preload	–	ARRAY3 starts tile3.
41	–	–	–	tile3 preload	ARRAY4 starts tile3 (3-cycle stagger).
42–58	continue +16 stride	same	same	same	Steady tile3 operation.

TABLE VIII
 x_t INPUT SCHEDULING ALIGNED WITH THE WAVEFRONT TILE SWITCH ACROSS SUB-ARRAYS.

Cycle	Array1	Array2	Array3	Array4	Description
1	xt[0:3]	–	–	–	ARRAY1 begins tile1 (xt block0).
2	xt[0:3]	xt[0:3]	–	–	ARRAY2 joins tile1.
3	xt[0:3]	xt[0:3]	xt[0:3]	–	ARRAY3 joins tile1.
4	xt[0:3]	xt[0:3]	xt[0:3]	xt[0:3]	ARRAY4 joins tile1; steady begins.
5–16	xt[0:3]	xt[0:3]	xt[0:3]	xt[0:3]	tile1 steady-state.
17	xt[4:7]	xt[0:3]	xt[0:3]	xt[0:3]	ARRAY1 starts tile2 (next row-block).
18	xt[4:7]	xt[4:7]	xt[0:3]	xt[0:3]	ARRAY2 switches to tile2.
19	xt[4:7]	xt[4:7]	xt[4:7]	xt[0:3]	ARRAY3 switches to tile2.
20	xt[4:7]	xt[4:7]	xt[4:7]	xt[4:7]	ARRAY4 switches; tile1 finishes.
21–33	xt[4:7]	xt[4:7]	xt[4:7]	xt[4:7]	tile2 steady-state.
34	xt[8:11]	xt[4:7]	xt[4:7]	xt[4:7]	ARRAY1 starts tile3.
35	xt[8:11]	xt[8:11]	xt[4:7]	xt[4:7]	ARRAY2 switches.
36	xt[8:11]	xt[8:11]	xt[8:11]	xt[4:7]	ARRAY3 switches.
37	xt[8:11]	xt[8:11]	xt[8:11]	xt[8:11]	ARRAY4 switches; tile2 ends.

resulting in a constant 12-column spacing between adjacent arrays. Table VI summarizes the per-array progression; and Table VII validates the constant 12-column spacing.

x_t input scheduling and waveform tile switch: The input vector x_t is streamed from xt_buf in 4-element blocks. During pipeline fill (cycles 1–4), ARRAY1 starts first and ARRAY2/3/4 join sequentially; in steady state, all arrays consume the same x_t block for the active tile. When moving to the next tile, the x_t block update is aligned with the weight schedule and propagates as a waveform across the arrays, minimizing global bubbles. Table VIII details the x_t schedule and matches the tile-switch cycles in Table V.

Overall, the $4 \times 4 \times 4$ pipelined array provides a favorable balance among DSP usage, bandwidth demand, latency, and reuse. However, the compromise shifts complexity to the memory subsystem. The next subsection therefore focuses on the memory-access design and compares single-port versus dual-port organizations in terms of power and resource cost.

B. Interleaved Memory Bank Design

Sustaining the $4 \times 4 \times 4$ pipeline MVM array in steady state requires the weight buffer (WBUF) to deliver stall-free parallel bandwidth, where four sub-arrays fetch one 4×4 column block per cycle. This section formalizes two conflict types and

derives single-port and dual-port realizations under a unified modulo-unrolling mapping [7].

Conflict model: Space-conflict captures same-cycle port contention when multiple arrays access the same bank. A single-port bank supports at most one read per cycle, hence all four arrays must hit distinct banks per cycle. A dual-port bank supports up to two reads per cycle, allowing two arrays to share one bank.

Temporal-conflict captures cross-cycle reuse hazards under a finite read latency L . A sufficient safety condition is

$$\text{bank reuse distance} \geq L, \quad (5)$$

which prevents issuing a new access to a bank before prior reads have been safely resolved in the pipeline.

Modulo-unrolling mapping derived from the array dataflow: Weights are accessed in 4-column blocks, each corresponding to a 4×4 weight block. Define

$$\text{block_id} = \left\lfloor \frac{\text{col}}{4} \right\rfloor, \quad n \in \{0, 1, 2, 3\}. \quad (6)$$

The schedule enforces a 12-column spacing between adjacent arrays within the same cycle, yielding a block-domain offset

$$\text{block_offset} = \frac{12}{4} = 3. \quad (7)$$

Therefore, the four arrays request

$$\text{block_id}, \text{block_id} + 3, \text{block_id} + 6, \text{block_id} + 9 \quad (8)$$

TABLE IX
POST-SYNTHESIS RESOURCE AND POWER COMPARISON BETWEEN
SINGLE-PORT AND DUAL-PORT WBUF ORGANIZATIONS.

Metric	Single-port	Dual-port
Bank count	12	6
Top-level BRAM tiles	49	46
WBUF BRAM tiles	48	45
DSP blocks	64	64
Dynamic power (W)	0.971	0.682
Static power (W)	0.626	0.624
Total on-chip power (W)	1.597	1.306

within a cycle. We adopt the modulo-unrolling mapping

$$\text{bank_id} = (\text{block_id} + 3n) \bmod N_{\text{bank}} \quad (9)$$

which provides periodic, hardware-friendly addressing while preserving the fixed inter-array spacing property for conflict analysis.

Single-port design by increasing the bank count: For single-port banks, eliminating space-conflict requires pairwise distinct bank IDs in the same cycle, i.e.,

$$3(n_1 - n_2) \not\equiv 0 \pmod{N_{\text{bank}}}, \quad \forall n_1 \neq n_2. \quad (10)$$

With four arrays and $\text{block_offset} = 3$, selecting $N_{\text{bank}} = 12$ satisfies this constraint robustly and yields a regular round-robin placement. Each bank stores every 12th 4-column block in a round-robin interleaving, and The runtime timeline is provided in Appendix A (Table XI), demonstrating that after warm-up four distinct banks are activated per cycle.

Dual-port design by exploiting two reads per bank per cycle: Dual-port banks relax the same-cycle constraint to “no more than two reads per bank per cycle,” while still requiring temporal safety against the effective latency L . With $N_{\text{bank}} = 6$, the per-cycle accesses collapse into two active banks per cycle, each serving exactly two reads through deterministic array pairing. Blocks are interleaved round-robin across six banks, and Table XII in Appendix A shows the bank-pair rotation $\{0, 3\} \rightarrow \{1, 4\} \rightarrow \{2, 5\}$. The reuse distance in this rotation is two cycles; therefore, the schedule is temporally safe when $L \leq 2$.

BRAM utilization and power implications: IX shows the single-port design uses 49 BRAM tiles at top level (48 in WBUF), while the dual-port design uses 46 (45 in WBUF) due to reduced bank replication. Power also favors dual-port: single-port consumes 1.597 W total (0.971 W dynamic, 0.626 W static) versus 1.306 W (0.682 W dynamic, 0.624 W static), consistent with lower memory/interconnect switching. Therefore, the dual-port WBUF offers a better BRAM-power trade-off without degrading throughput and is selected as the default.

C. Nonlinear Layer Implementation

To realize the sigmoid nonlinearity $\sigma(x) = 1/(1 + e^{-x})$ with low FPGA overhead, we implement a lookup-table (LUT) approximation. The module consumes signed Q8.8 inputs (16-bit) and produces unsigned Q0.16 outputs (16-bit). Inputs are first clamped to $[-4, +4]$. Importantly, this interval is selected

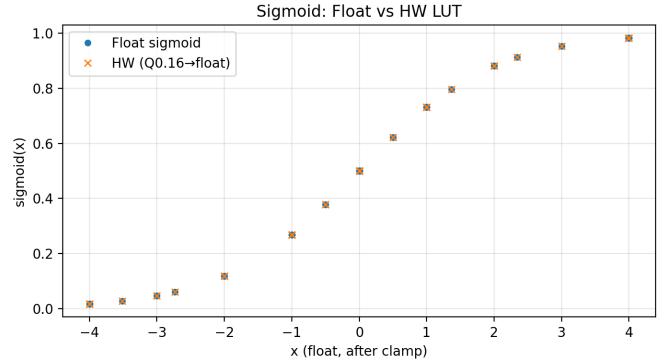


Fig. 4. Sigmoid approximation accuracy: floating-point sigmoid vs. HW LUT outputs.

based on empirical workload statistics: sampled dt_{proj} values before the sigmoid are concentrated within this range, which avoids over-provisioning the LUT in saturation regions while keeping the table size compact.

After clamping, the address is generated by a direct fixed-point shift. Since $[-4, +4]$ corresponds to $[-1024, 1023]$ in Q8.8, we compute

$$\text{addr} = x_{\text{clamp}} + 1024, \quad (11)$$

to obtain an index in $[0, 2047]$, enabling a 2048-entry LUT that uniformly covers the effective domain. Fig. 4 compares the floating-point sigmoid against the hardware LUT outputs (converted from Q0.16), showing close agreement at the sampled points, thereby validating the chosen clamp range and table resolution.

D. SSM Control and Fine-grained Pipelining

To reduce inter-module coupling and improve scalability, we adopt an AXI-stream-like ready/valid interface and insert lightweight FIFOs between adjacent operators, following the modular streaming philosophy of LightMamba [8]. Under this semantics, a FIFO acts as a standardized boundary for rate matching and timing decoupling. Crucially, the unified interface also simplifies system evolution: extending from an SSM subgraph toward a full Mamba pipeline becomes a matter of composing compliant modules with similar AXI-Stream interfaces, which improves project maintainability and integration robustness.

Within this control paradigm, we examine the trade-off between reconfigurable and fine-grained pipelines. Many Mamba/SSM accelerators favor reconfigurable datapaths to reduce resource usage [3]–[5], but increases end-to-end waiting time. In contrast, LightMamba advocates fine-grained streaming, where each MAC tile is immediately forwarded to the sigmoid and element-wise update (EWM/EWA) stages. In our throughput analysis with $N = 64$ tiles, the fine-grained schedule reduces latency from $T_A = 29N$ to $T_B = 22N + 7$, i.e., from 1856 to 1415 cycles (23.8% reduction) while adds only about 12 DSPs per SSM compute path, making the latency gain well justified. Therefore, this project ultimately selects the fine-grained, FIFO-based AXI-stream control scheme.

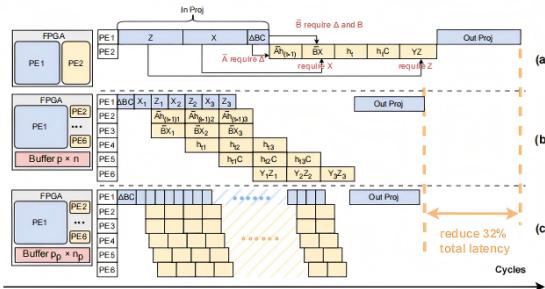


Fig. 5. Fine-grained streaming schedule from LightMamba [8].

TABLE X
POST-SYNTHESIS UTILIZATION AND POWER SUMMARY FOR THE INTEGRATED SSM MODULE AT 400 MHZ.

Metric	Value
LUTs	6,244 (2.28%)
FFs	4,928 (0.90%)
BRAM tiles	52 (5.70%)
DSP blocks	76 (3.02%)
Bonded I/Os	136 (41.46%)
Total on-chip power	1.442 W
Dynamic power	0.817 W
Static power	0.625 W
I/O power (dynamic)	0.443 W (54%)
BRAM power (dynamic)	0.089 W
Signals power (dynamic)	0.081 W
Clocks power (dynamic)	0.078 W
Logic power (dynamic)	0.073 W
DSP power (dynamic)	0.053 W

V. CONCLUSION

This work targets the SSM state-update hotspot in Mamba for indoor localization (LuViRA) and presents a fully synthesizable FPGA accelerator subsystem with an SSM-centric streaming datapath. At 400 MHz, the design closes timing with a compact footprint (76 DSPs, 6.2k LUTs; 3.0% and 2.3% of the device) and uses 52 BRAM tiles (5.7%) to support fully on-chip buffering for streaming MVM and recurrent state update. Post-synthesis power is estimated at 1.442 W, where dynamic power is dominated by top-level I/O toggling, as the current deliverable implements the SSM module without a full-system wrapper. In the master's thesis, we will integrate the module into a complete Mamba pipeline to keep data on-chip and re-estimate power using realistic switching activity.

Overall, the results show that an SSM-centric accelerator can achieve high frequency on FPGA with modest resources. Key enablers include: (i) a primitive-based mapping (MAC/EWA/EWM) that simplifies control; (ii) a pipelined MVM backbone with structured reduction; (iii) bank-aware, deterministic BRAM access; and (iv) LUT-based sigmoid plus FIFO/ready-valid streaming for robust composition and backpressure handling.

VI. REFLECTIONS ON THIS COURSE

This course trained me in practical research methodology: surveying and critiquing related work, forming testable hypotheses, and iterating on design choices through evidence and discussion. We started from a defined plan with the baseline of implementing the Mamba SSM hardware module. Through literature review and continuous group feedback, we went beyond the initial target: we completed the SSM design and performed a comprehensive analysis of MVM computation, memory-access strategies, and system-architecture trade-offs. The resulting solution is tailored to the indoor-localization workload and is documented in both a public GitHub repository and this report for reproducibility. Finally, participating in the IES Group Meeting gave me a firsthand view of how research is conducted and communicated within the department, which was a valuable and motivating experience.

APPENDIX A BANK ACCESS TIMELINES

TABLE XI
TIMELINE OF BANK ACCESSES FOR $N_{\text{BANK}} = 12$ (SINGLE-PORT).

Cycle	A1 → bank	A2 → bank	A3 → bank	A4 → bank	Banks Active
1	bank0	—	—	—	{0}
2	bank4	bank1	—	—	{4,1}
3	bank8	bank5	bank2	—	{8,5,2}
4	bank0	bank9	bank6	bank3	{0,9,6,3}
5	bank4	bank10	bank7	bank1	{4,10,7,1}
6	bank8	bank11	bank2	bank5	{8,11,2,5}
7	bank0	bank3	bank6	bank9	{0,3,6,9}
8	bank4	bank7	bank10	bank1	{4,7,10,1}
9	bank8	bank11	bank2	bank5	{8,11,2,5}
10	bank0	bank3	bank6	bank9	{0,3,6,9}
11	bank4	bank7	bank10	bank1	{4,7,10,1}
12	bank8	bank11	bank2	bank5	{8,11,2,5}

TABLE XII
TIMELINE OF BANK ACCESSES FOR $N_{\text{BANK}} = 6$ (DUAL-PORT).

Cycle	A1 → bank	A2 → bank	A3 → bank	A4 → bank	Banks Active
1	bank0	—	—	—	{0}
2	bank4	bank1	—	—	{1,4}
3	bank2	bank5	bank2	—	{2,5}
4	bank0	bank3	bank0	bank3	{0,3}
5	bank4	bank1	bank4	bank1	{1,4}
6	bank2	bank5	bank2	bank5	{2,5}
7	bank0	bank3	bank0	bank3	{0,3}
8	bank4	bank1	bank4	bank1	{1,4}
9	bank2	bank5	bank2	bank5	{2,5}
10	bank0	bank3	bank0	bank3	{0,3}
11	bank4	bank1	bank4	bank1	{1,4}
12	bank2	bank5	bank2	bank5	{2,5}

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