

Wireless Channel Measurements and Characterization in Industrial IoT Scenarios

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Abstract—Wireless Fidelity (Wi-Fi) communication technologies hold significant potential for realizing the Industrial Internet of Things (IIoT). In this paper, both Single-Input Single-Output (SISO) and polarized Multiple-Input Multiple-Output (MIMO) channel measurements are conducted in an IIoT scenario at the less congested Wi-Fi band, i.e., 5.5 GHz. The purpose is to investigate wireless characteristics of communications between access points and terminals mounted on automated guided vehicles as well as those surrounding manufacturing areas. For SISO channel measurements, statistical properties including the delay Power Spectral Density (PSD), path loss, shadowing fading, delay spread, excess delay, K-factor, and amplitude distribution of small-scale fading are analyzed and compared with those observed in an office scenario. For MIMO channel measurements, results show that there are multiple Dense Multipath Component (DMC) processes in the delay PSD. An estimation algorithm based on the algorithm for a single DMC process is proposed to effectively process the multi-processes data. Moreover, delay, angular, power, and polarization properties of DMCs are investigated and compared with those of specular multipath components. Furthermore, effects of DMCs on Singular Values (SVs) and channel capacities are explored. Ignoring DMCs can overestimate SVs and underestimate channel capacities.

Index Terms—IIoT scenarios, wireless channel measurements, channel characterization, specular multipath components, dense

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multipath components.

I. INTRODUCTION

ADVANCEMENTS in Internet of Things (IoT) technologies—identification [1], communication [2], [3], computation [4], sensing, etc.—have propelled Industrial IoT (IIoT) applications. IIoT enables the seamless integration of sensors, controllers, and various devices into industrial production processes, enhancing automation and efficiency. In manufacturing scenarios, Automated Guided Vehicles (AGVs), mobile robots, and robotic arms are indispensable. Hence, wireless networks are preferred for those mobile devices by offering flexible deployment, convenient maintenance, and low costs. Meanwhile, Customer Premises Equipment (CPE) can extend network accessibility, integrating legacy equipment into wireless networks.

Amidst wireless communication technologies, Wireless Fidelity (Wi-Fi) emerges as a versatile solution for industrial networks due to its utilization of unlicensed spectrum and the extensive existing infrastructure. The latest Wi-Fi 6 is specifically designed for high-density and high-capacity services. It operates seamlessly across 2.4 GHz and 5 GHz bands, leveraging advantages of each band. Notably, the 5 GHz band offers a larger number of non-overlapping channels and can therefore enhance network capacities and reduce interferences. Other newly introduced technologies such as orthogonal frequency-division multiple access, target wake time, etc., can significantly improve the spectral efficiency [5]. Therefore, strategic deployment of Wi-Fi 6 alongside CPE enables wireless connectivity of industrial devices. However, IIoT scenarios are characterized by higher ceilings, larger floor spaces, and more intricate obstructions [6]. Wireless communications between Access Points (APs) and CPE mounted on AGVs or production machinery can encounter intricate multipath effects. To successfully design and deploy Wi-Fi networks in IIoT scenarios, conducting channel measurements and characteristic analysis at Wi-Fi bands is necessary [7].

The existing channel measurements in IIoT scenarios are summarized in Table I. Basically, the measured frequency bands can be classified as five types, i.e., the Fifth Generation (5G) New Radio (NR) bands, not special bands, Industrial Scientific Medical (ISM) bands, Ultra-WideBand (UWB) bands, and Wi-Fi bands. For 5G NR bands, channel measurements were conducted at 3.5 GHz [8]–[10], 3.7 GHz [11], 3.75 GHz [12], 4.1 GHz [13], 4.9 GHz [14]–[16], and 28 GHz [11], [15]–[20]. The investigated channel

characteristics mainly focused on Path Loss (PL), Shadowing Fading (SF), Delay Spread (DS), delay Power Spectral Density (PSD), and Angular Spreads (ASs) at millimeter wave bands. For not special bands, Multiple-Input Multiple-Output (MIMO) channel measurements were conducted at 3 GHz [21], 1.35 GHz [22], and 1.3 GHz [23]. Results in [21] found that the power of Dense Multipath Components (DMCs) accounted for 23% to 70% of the total channel power and the reverberation time was nearly constant. In [22], polarized properties of Specular Multipath Components (SMCs) and DMCs in a large industrial hall were compared. Authors in [23] analyzed the delay PSD, Cross-Polarization Ratio (XPR), DMC power ratio, and reverberation time of different polarization pairs. These measurements highlighted a significant effect of DMCs on the total power and investigated the polarized properties of DMCs. However, angular properties of DMCs and their effects on the system performance are not explored. Besides, channel characteristics at these frequency bands cannot accurately describe those at Wi-Fi bands.

In terms of Wi-Fi frequency bands, i.e., 2.4–2.4845 GHz and 5.15–5.85 GHz, several channel measurements at ISM bands [24]–[28] and UWB bands [29], [30] covered part Wi-Fi bands. The interested ISM bands are 915 MHz, 2.45 GHz, and 5.8 GHz. Authors in [24] conducted Single-Input Single-Output (SISO) channel measurements at 5.8 GHz in various industrial environments and analyzed results about the PL, DS, and coherence bandwidth. In [25], frequency domain channel measurements were performed from 800 MHz to 2.7 GHz to study the PL, SF, and their effects on channel capacity. In [26]–[29], Virtual Antenna Arrays (VAAs) were employed to investigate the amplitude distribution of the Small-Scale Fading (SSF). The Salen–Valenzula (S–V) model was adopted in the UWB communication with parameters obtained from measurements. Authors in [30] performed SISO measurements at 3–8 GHz and channel properties including PL, SF, DS, and Excess Delay (ED) were analyzed. Authors in [31] performed three types of MIMO channel measurements at 2.37 GHz and 5.4 GHz to obtain statistical distributions of the eight Large-Scale Parameters (LSPs), such as K-factor (KF), DS, etc. In [32], MIMO channel measurements were conducted in an aircraft manufacturing plant at 2.4 GHz and 5.4 GHz. Two exponential functions were employed to model the delay PSD. However, antenna heights in these channel measurements are nearly the same, while [28] and [31] imitate communications between AP and terminals. Besides, investigated statistical properties of these channel measurements are incomplete and exclude characteristics of DMCs.

In summary, existing channel measurements in IIoT scenarios mainly focus on characterizing 5G NR bands, while only a few works are related to Wi-Fi bands, especially the less congested 5 GHz Wi-Fi band (5.15–5.85 GHz). Antenna heights in these channel measurements are nearly the same, which cannot provide an accurate analysis of channel characteristics for the scenario between APs and industrial terminals, particularly in AP-AGV scenario. In the AGV communication situation, the receiving antenna is set at a very low height, leading to more severe multipath fading compared to that at higher antenna heights. In addition, current investigations of

channel characteristics at 5 GHz Wi-Fi bands are incomplete, particularly in studying the LSF, angular, polarization, and DMCs characteristics. To fill the above gaps, we conduct both SISO and MIMO channel measurements at 5.5 GHz in an automobile manufactory. Two typical Wi-Fi application scenarios are considered, i.e., communications between APs and industrial CPEs installed on AGVs and manufacturing equipment. Based on channel measurements, a comprehensive characterization is conducted and compared with results in an indoor office scenario [33]. The main contributions and novelties of this paper are summarized as follows.

- 1) Both SISO and MIMO channel measurements and characteristics analysis are conducted at 5.5 GHz between APs and terminals in IIoT application scenarios. The channel measurement dataset, along with channel characterization, not only furnishes parameters essential for IIoT channel models but also provides guidance for designing and optimizing Wi-Fi systems in IIoT scenarios.
- 2) A novel estimation algorithm is proposed to accommodate the multiple DMC processes in the delay PSD, which is a unique property in the measured IIoT scenario. The first-order difference method is applied to detect transition points in the slope of each process and base delays are normalized so that they can be iterated under an equivalent number of frequency points. The proposed algorithm enhances the power extraction efficiency from 79% to 99.6%, thus exhibiting superior performance over the existing algorithms with a single DMC process.
- 3) A comprehensive channel characteristic analysis is conducted. For SISO channel measurements, statistical properties including the delay PSD, PL, SF, DS, ED, KF, and amplitude distribution of SSF are studied. Regarding MIMO channel measurements, the delay, angular, power, and polarization characteristics of SMCs and DMCs are analyzed and compared. Furthermore, effects of DMCs on Singular Values (SVs) and channel capacities are explored. Results show that incorporating both SMCs and DMCs leads to a decrease in SVs and an increase in channel capacities compared to results with only SMCs.

The rest of this paper is structured as follows. Section II outlines the channel measurement campaign in IIoT scenarios. In Section III, the method of estimating channel parameters of SMCs and DMCs is described. Measurement results and analysis are presented in Section IV. Section V draws conclusions of this paper.

II. CHANNEL MEASUREMENTS

A. Measurement Environment

Channel measurements are performed by a time domain channel sounder, as depicted in Fig. 1. It includes a Transmitter (Tx) and a Receiver (Rx) and more detailed information of this sounder can be found in [33].

The measurement campaigns are conducted in a large automobile manufactory with a size of $156 \times 100 \times 14.6 \text{ m}^3$. This manufactory can be primarily divided into an idle section and the other section comprising three assembly lines. Three

TABLE I
SUMMARY OF CHANNEL MEASUREMENTS IN IIOT SCENARIOS.

Ref.	Environment	Frequency (GHz)	Bandwidth (MHz)	Antenna Configuration	Antenna Height (m)	Channel Properties
[8]	Automobile assembly factory	3.5	160	64×64 MIMO	Tx: 4.1, Rx: 1.5	Delay PSD, DS, ED, ASD, ASA, ESD, ESA, channel rank
[9]	Large workshop	3.5	160	64×64 MIMO	Tx: 3	Delay PSD, amplitude of SSF, DS
[10]	Machine workshop	3.4–3.8	400	SIMO (VAA)	/	Power decay rate, delay PSD, DS
[11]	Machining workshop hall	3.7, 28	2000	3:7: SISO 28: SIMO (VAA)	Tx: 1.85, Rx: 1.44	PL, SF, DS delay PSD, angular PSD, ASA
[12]	AGV to AGV	3.75	100	SISO	Tx, Rx: 0.8	Received power, DS
[13]	Manufacturing plant	4.1	100	SISO	Tx: 3.7, Rx: 1.5	PL, SF, DS, KF
[14]–[16]	Factory	4.9 28	100 800	SISO	Tx: 2.5, Rx: 2.5 Tx: 2.5, Rx: 1.9 Tx: 1.9, Rx: 1.9 Tx: 1.9, Rx: 0.9	PL, SF, DS, KF
[17]	Fiber optic cable laboratory	28	2400	SISO & SIMO (VAA)	Tx, Rx: 0.84 Tx, Rx: 1.6	PL, SF, DS, angular PSD, ASA
[18]	Japanese sake factory	28	100	SISO & SIMO (VAA)	Tx: 2.5, Rx: 1.8	PL, SF, DS, angular PSD, ASA, ESD
[19]	Manufacturing zone	28	2000	SIMO (VAA)	Rx: 1.6	PL, SF, DS, ASA, XPR
[20]	Circle-shaped machine hall	28	2000	SIMO (VAA)	Tx: 7, Rx: 1.7&4	PL, SF, DS, delay PSD angular PSD, ASD, ASA
[21]	Workshop for reparation	3	100	8×8 MIMO (VAA)	Tx: 1.5, Rx: 1.5	DMC power ratio and reverberation time
[22]	Large industrial hall	1.3	22	12×12 MIMO (VAA)	Tx: 1.6, Rx: 1.6	DS, XPR, DMC power ratio
[23]	Flower auction warehouse	1.35	80	8×8 MIMO	Tx: 6, Rx: 2	DMC reverberation time, XPR, delay PSD, DMC power
[24]	Warehouse, manufacturing shop, mechanical workshop	5.8	600	SISO	Tx, Rx: 1.9 Tx: 1.57, Rx: 1.85 Tx: 1.57, Rx: 1.4	PL, DS, coherence bandwidth
[25]	Assembly shop, electronics room, mechanical room	0.8–2.7	1900	SISO	Tx: 1.8, Rx: 1.8	PL, SF, channel capacity
[26]	Assembly shop, electronics room, mechanical room	0.8–2.7	1900	5×18 MIMO (VAA)	Tx: 1.8, Rx: 1.8	Delay PSD, power decay rate, amplitude of SSF
[27]	Machinery room	2–6	4000	9×27 MIMO (VAA)	/	Power decay rate
[28]	Production rooms	0.8–4	3200	4×12 MIMO (VAA)	Tx: 6, Rx: 2	Power decay rate, amplitude of SSF
[29]	Factory hall	3.1–10.6	7500	7×7 MIMO (VAA)	Tx: 1, Rx: 1	Power decay rate, amplitude of SSF
[30]	Smart production lab	3–8	5000	SISO	Tx, Rx: 1–2	PL, SF, DS, ED
[31]	Five factory halls	5.4 2.37	200 50	32/30×50 MIMO 32×56 MIMO	Tx: 2–8, Rx: 2	SF, DS, KF, ASD, ASA, ESD, ESA, XPR
[32]	Aircraft manufacturing plant	2.4, 5.4	100 & 500	4×4 MIMO (VAA)	Tx: 1.5, Rx: 1.5	Delay PSD, DS
This paper	Automobile manufactory	5.5	320	SISO & 32×64 MIMO	Tx: 4.8, Rx: 0.3 & 1 Tx: 4.5, Rx: 1.35	SISO: delay PSD, PL, SF, DS, ED, KF, and amplitude of SSF MIMO: delay, angular, power, and polarization properties of SMCs and DMCs, effects of DMCs on SVs and capacity

channel measurement cases are conducted in both Line-Of-Sight (LOS) and Non-LOS (NLOS) scenarios within the area of assembly lines. Due to the restrictions, photography was not permissible during measurements. Fig. 2 presents a layout of the measurement area and offers a concise depiction. Each assembly line is $156 \times 14 \text{ m}^2$ and consists of several operating islands equipped with operating platforms, mechanical arms, slide rails, and metal materials. Between the assembly lines, there are pedestrian walkways with a width of 5 m. On one side of each assembly line, metal pillars are evenly distributed and APs are spaced on these metal pillars. In addition, numerous irregularly shaped steel grids exist on the ceiling and the ground floor is very smooth.

B. Measurement Setup

For SISO channel measurements, two identical omnidirectional antennas are used at Tx and Rx sides to obtain characteristics of the PL, DS, ED, etc. The omnidirectional antenna works at 2–8 GHz with a gain of 0 dBi. The

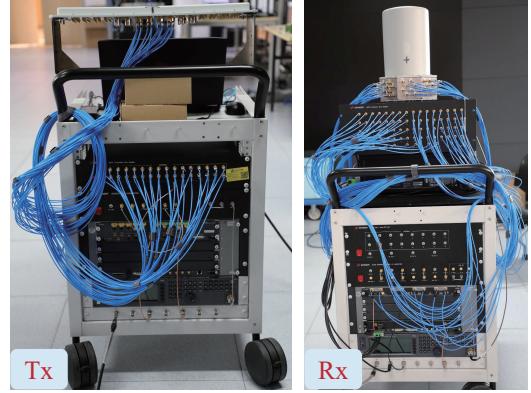


Fig. 1. Time domain 32×64 MIMO channel sounder.

radiation pattern of the omnidirectional antenna exhibits a wide elevation beam with a 3 dB beamwidth of 140°. Here, omnidirectional antennas are employed to analyze propagation

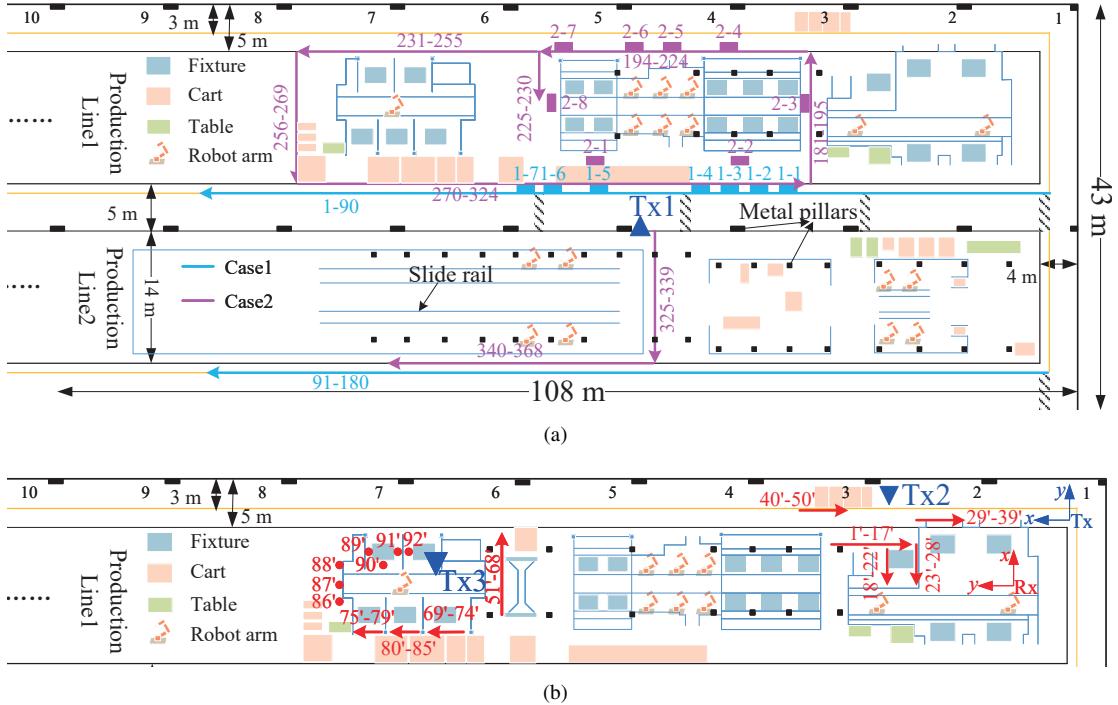


Fig. 2. Measurement positions of (a) SISO and (b) MIMO channel measurements in IIoT scenarios.

channel characteristics independent of the antenna directionality. The obtained channel parameters, such as DS and KF, serve as vital inputs to IIoT channel models. For MIMO channel measurements, the Tx antenna consists of a 4×4 dual-polarized Uniform Planar Array (UPA) and the Rx antenna is a 4×8 dual-polarized Uniform Cylindrical Array (UCA). Both Tx and Rx antenna arrays work at 5.15–5.85 GHz. Antenna elements are spaced with an interval of half the wavelength at 5.5 GHz. Rayleigh distances of Tx and Rx antenna arrays are 0.4912 m and 0.8006 m, satisfying the far-field assumption. The Tx and Rx antenna gains are 8.8 dBi and 8 dBi, respectively. The front-to-back gain, axial XPR (@ 0°), and sector XPR (@ $\pm 60^\circ$) of each antenna element at both sides are 17 dB, 15 dB, and 10 dB, respectively.

C. Measurement Cases

In order to explore comprehensive channel characteristics at Wi-Fi frequency bands in IIoT scenarios, both SISO and polarized MIMO channel measurements are conducted. The carrier frequency is set as 5.5 GHz, which is an unlicensed Wi-Fi band. Considering the obvious multipath effect in IIoT scenarios and capability of the channel sounder, the measurement bandwidth is set as 320 MHz to guarantee the high delay resolution. Two typical communication scenarios involving interactions between APs and terminals are considered. The first scenario focuses on wireless communications between an AP and the CPE installed on AGVs. The measurement route aligns with the AGV's actual moving trajectories to capture realistic channel conditions. The second scenario is the communication link between the AP and various terminals scattered around the manufacturing area. Therefore, measurement points are distributed across the manufacturing

area. During channel measurements, the Tx antenna is used to simulate the AP, while the Rx is used to imitate industrial terminals. Totally, there are three measurement cases and they provide a comprehensive evaluation of the wireless network at Wi-Fi bands in IIoT scenarios.

1) *Case 1:* To explore channel properties of communications between APs and the CPE mounted on AGVs, SISO channel measurements are carried out. The Rx antenna is set at a height of 0.3 m to simulate actual AGV conditions, while the Tx antenna is positioned at a height of 4.8 m, similar to the height of an actual AP. Measurement positions are distributed along two separate routes, each with a length of 90 m. The distance between adjacent Rx positions is 1 m, resulting in a total of 180 Rx positions. To analyze the power fluctuations when varying the Rx positions across several wavelength ranges, there are 7 locally amplified positions, designated as RxA1-1 to RxA1-7 in Fig. 2. The Rx antenna is moved with step size of 0.2 m (approximately four wavelengths at 5.5 GHz) to form a 5×10 UPA, enabling the study of amplitude distribution for SSF.

2) *Case 2:* SISO channel measurements are performed to investigate wireless channel characteristics between APs and terminals suited in the manufacturing area. Heights of Tx and Rx antennas are set as 4.8 m and 1 m, respectively. The Tx position in Case 2 remains consistent with that in Case 1, i.e., Tx1 in Fig. 2. A total of 188 Rx positions are distributed around the manufacturing area, with a spacing of 1 m between adjacent Rx positions. The Three-Dimensional (3D) distances of all positions are 6–48.1 m in Case 1, 4.6–40.9 m in Case 2, and 3.1–39.7 m in office scenarios. Based on the antenna height and antenna beamwidth, the covered 3D distance between the Tx and Rx is larger than 5.1 m. Hence,

TABLE II
CONFIGURATIONS FOR THREE MEASUREMENT CASES.

Cases	Scenarios	Antenna Type	Antenna Height (m)	Measurement Positions
1	AGV's trajectory	Omnidirectional antennas (SISO)	Tx: 4.8 Rx: 0.3	Tx: 1 Rx: 180, RxA: 7
2	Manufacturing area	Omnidirectional antennas (SISO)	Tx: 4.8 Rx: 1	Tx: 1 Rx: 188, RxA: 8
3	Manufacturing area	Tx: UPA Rx: UCA	Tx: 4.5 Rx: 1.35	Tx: 2 Rx: 92

we ignore these positions with 3D distances smaller than 5.1 m in the analysis. Similarly, there are 8 locally amplified positions, indicated as RxA2-1 to RxA2-8 in Fig. 2.

3) *Case 3*: To study the angular and polarized characteristics of wireless channels between APs and terminals around the manufacturing area, 32×64 polarized MIMO channel measurements are conducted. Antenna heights of the Tx and Rx are 4.5 m and 1.35 m, respectively. There are two Tx positions, with Tx2 located adjacent to a wall and 50 LOS positions distributed on one side of the Tx position. Meanwhile, Tx3 is situated at the center of an operation island and surrounded by 42 LOS positions. To distinguish position numbers in Case 1 and Case 2, the numbering of 92 positions in Case 3 is designated as Rx1'-Rx92'. In addition, the local coordinate systems of Tx and Rx antennas are provided in Fig. 2. Three measurement cases are summarized in Table II.

III. MEASUREMENT DATA PROCESSING

During the measurement data processing, the Channel Impulse Response (CIR) is firstly obtained by calibrating out effects of the system response from the raw measurement data. For SISO channel measurements, the peak search algorithm is used to extract MultiPath Components (MPCs) from the delay PSD with a threshold determined by the maximum power and noise floor. Then, the received power is estimated by summing the power of all MPCs' path gains. More details can be found in [33]. For MIMO channel measurements, SMCs and DMCs are estimated to describe the wireless channel. The channel parameter estimation is based on the Maximum Likelihood (ML) principle. For SMCs, the state-of-the-art dual-polarized Space-Alternating Generalized Expectation-maximization (SAGE) algorithm [34] is employed. Channel parameters of each path can be extracted, including the amplitude, delay, Elevation angle Of Arrival (EoA), Azimuth angle Of Arrival (AoA), Elevation angle Of Departure (EoD), and Azimuth angle Of Departure (AoD). Regarding DMCs, their parameters in the delay PSD and angular PSD are estimated by a Levenberg-Marquardt algorithm with Fisher scoring. Traditionally, DMCs in existing channel measurements are estimated by a single DMC process within the delay PSD model. However, measurement results in IIoT scenarios reveal that there are multiple independent DMC processes. Therefore, the approach in [35] is extended to accommodate and effectively process such multi-process measurement data in IIoT scenarios.

A. SMCs

Let $\mathbf{H}_{\text{meas}}(\mathbf{f}) \in \mathbb{C}^{M_R \times M_T \times M_f}$ denote the measured channel transfer function matrix, which is obtained by Fast Fourier Transform (FFT) of CIR $\mathbf{h}_{\text{meas}}(\tau) \in \mathbb{C}^{M_R \times M_T \times M_f}$. Here, $M_R = 64$, $M_T = 32$, and M_f are the number of Rx antennas, Tx antennas, and frequency points, respectively. Vectors of frequency points and delay indices are denoted by $\mathbf{f} \in \mathbb{R}^{M_f}$ and $\tau \in \mathbb{R}^{M_f}$, respectively. The complex and real domains are represented by \mathbb{C} and \mathbb{R} . SMCs are characterized by the parameter set $\Theta_S = [\theta_1, \theta_2, \dots, \theta_L]$, where $\theta_l = [\theta_l^R; \phi_l^R; \theta_l^T; \phi_l^T; \tau_l; \text{vec}(\alpha_l)]$. Here, symbols θ_l^R , ϕ_l^R , θ_l^T , ϕ_l^T , and τ_l denote the EoA, AoA, EoD, AoD, and propagation delay, respectively. Besides, $\alpha_l = [\alpha_l^{VV}, \alpha_l^{VH}, \alpha_l^{HV}, \alpha_l^{HH}] \in \mathbb{C}^{2 \times 2}$ is the complex amplitude matrix of four polarization modes, and $\text{vec}(\cdot)$ denotes the vectorization operation. The estimated dual-polarized transfer function matrix of SMCs can be characterized by the superposition of L individual paths as

$$\hat{\mathbf{H}}_S(\mathbf{f}; \Theta_S) = \sum_{l=1}^L \mathbf{F}_R(\theta_l^R, \phi_l^R) \alpha_l \mathbf{F}_T(\theta_l^T, \phi_l^T)^T e^{j2\pi f \tau_l}. \quad (1)$$

In (1), radiation patterns of Rx and Tx antenna arrays are represented by $\mathbf{F}_R(\theta_l^R, \phi_l^R) \in \mathbb{C}^{M_R \times 2}$ and $\mathbf{F}_T(\theta_l^T, \phi_l^T) \in \mathbb{C}^{M_T \times 2}$, respectively. The transpose operation is denoted by $(\cdot)^T$. A comprehensive description of the initialization and iteration process can be found in [34]. In a word, the estimated parameters $\hat{\Theta}_S$ maximize the likelihood function

$$\hat{\Theta}_S = \arg \max_{\Theta_S} \left\{ -\left\| \text{vec}\left\{ \mathbf{H}_{\text{meas}}(\mathbf{f}) \right\} - \text{vec}\left\{ \hat{\mathbf{H}}_S(\mathbf{f}; \Theta_S) \right\} \right\|_{\text{F}}^2 \right\} \quad (2)$$

where $\|\cdot\|_{\text{F}}$ is the Frobenius norm.

B. DMCs

The measured channel transfer function matrix of DMCs $\mathbf{H}_{D,\text{meas}}(\mathbf{f}) \in \mathbb{C}^{M_R \times M_T \times M_f}$ is calculated by subtracting SMCs from the measurement data as

$$\mathbf{H}_{D,\text{meas}}(\mathbf{f}) = \mathbf{H}_{\text{meas}}(\mathbf{f}) - \hat{\mathbf{H}}_S(\mathbf{f}; \Theta_S). \quad (3)$$

The measured covariance matrix is represented by

$$\mathbf{R}_{D,\text{meas}} = \text{vec}(\mathbf{H}_{D,\text{meas}}(\mathbf{f})) \text{vec}(\mathbf{H}_{D,\text{meas}}(\mathbf{f}))^H \quad (4)$$

where $(\cdot)^H$ is the Hermitian transpose. The estimation of DMCs is based on correlation matrices in frequency and spatial domains. The delay PSD is characterized by an exponential decay distribution as [35]

$$\Psi(\tau) = \begin{cases} \alpha_0, & \tau < \tau_d \\ \alpha_1/2, & \tau = \tau_d \\ \alpha_1 e^{-B_d(\tau - \tau_d)}, & \tau > \tau_d \end{cases} \quad (5)$$

where B_d , α_1 , α_0 , and τ_d are the power decay rate, maximum power, minimum power, and base delay related to the Tx-Rx distance, respectively. The parameter vectors describing correlation matrices of K uncorrelated DMC processes in the delay domain are denoted as $\boldsymbol{\theta}_F^k = [\alpha_1^k, B_d^k, \tau_d^k]$. Hence, the covariance matrix in the frequency domain is given by the sum

of covariance matrices of K independent DMC processes and white noise as

$$\hat{\mathbf{R}}(\boldsymbol{\theta}_F) = \alpha_0 \mathbf{I} + \text{toep} \left(\boldsymbol{\kappa}(\boldsymbol{\theta}_F), \boldsymbol{\kappa}(\boldsymbol{\theta}_F)^H \right) \in \mathbb{C}^{M_f \times M_f} \quad (6)$$

where \mathbf{I} is an identity matrix and $\text{toep}(\cdot)$ is the Toeplitz function. Besides, the sample of frequency correlation matrix is written as $\boldsymbol{\kappa}(\boldsymbol{\theta}_F) = \sum_{k=1}^K \boldsymbol{\kappa}(\boldsymbol{\theta}_F^k)$ and the k -th component is calculated similar to [35].

The joint azimuth–elevation angular PSD is fitted by the multimodal Von Mises-Fisher (VMF) distribution and an example at the Rx side is given by

$$f(\vartheta, \varphi; \boldsymbol{\theta}_A^R) = \sum_{q=1}^Q \epsilon_q^R \frac{(\kappa_q^R)^{\frac{1}{2}}}{(2\pi)^{\frac{3}{2}} I_{\frac{1}{2}}(\kappa_q^R)} e^{\kappa_q^R \mu_q^R \Omega(\vartheta, \varphi)} \quad (7)$$

where angular parameters at the Rx side are represented by $\boldsymbol{\theta}_A^R = [\boldsymbol{\theta}_{A,1}^R; \dots; \boldsymbol{\theta}_{A,Q}^R]$ and $\boldsymbol{\theta}_{A,q}^R = [\vartheta_q^R, \varphi_q^R, \kappa_q^R, \epsilon_q^R]$. Here, Q is the number of components and ϵ_q^R is the proportion of each component with $\sum_{q=1}^Q \epsilon_q^R = 1$. Besides, $\kappa_q^R \geq 0$ is the concentrated parameter of DMCs and $\boldsymbol{\mu}_q^R = [\cos(\vartheta_q^R) \cos(\varphi_q^R), \cos(\vartheta_q^R) \sin(\varphi_q^R), \sin(\vartheta_q^R)]$ is the direction of arrival angle determined by the AoA φ_q^R and EoA ϑ_q^R . Symbol $I_{\frac{1}{2}}(\cdot)$ is the modified Bessel function of the first kind and the spherical unit vector is denoted by $\boldsymbol{\Omega}(\vartheta, \varphi) = [\cos(\vartheta) \cos(\varphi), \cos(\vartheta) \sin(\varphi), \sin(\vartheta)]^T$. Under the condition of $\kappa_q^R = 0$, the angular PSD reduces to a uniform distribution. The angular PSD and parameters at the Tx side are similar to those at the Rx side and will not be explained in detail.

It is assumed that the covariance matrix of DMCs can be factorized into a Kronecker product. Hence, the estimated covariance matrix of DMCs is represented by

$$\hat{\mathbf{R}}(\boldsymbol{\Theta}_D) = \hat{\mathbf{R}}(\boldsymbol{\theta}_F) \otimes \hat{\mathbf{R}}(\boldsymbol{\theta}_A^R) \otimes \hat{\mathbf{R}}(\boldsymbol{\theta}_A^T) \quad (8)$$

where \otimes is the Kronecker product. Besides, $\hat{\mathbf{R}}(\boldsymbol{\theta}_A^T) \in \mathbb{C}^{M_T \times M_T}$ and $\hat{\mathbf{R}}(\boldsymbol{\theta}_A^R) \in \mathbb{C}^{M_R \times M_R}$ indicate the estimated covariance matrices in the angular domain at both Tx and Rx sides. The optimization of DMC parameters $\boldsymbol{\Theta}_D = [\boldsymbol{\theta}_F; \boldsymbol{\theta}_A^R; \boldsymbol{\theta}_A^T]$ can be performed by maximizing the log-likelihood function as [36]

$$\hat{\boldsymbol{\Theta}}_D = \arg \max_{\boldsymbol{\Theta}_D} \left\{ -\ln (\det(\hat{\mathbf{R}}(\boldsymbol{\Theta}_D))) - \text{tr}(\hat{\mathbf{R}}(\boldsymbol{\Theta}_D)^{-1} \mathbf{R}_{D,\text{meas}}) \right\} \quad (9)$$

where $\det(\cdot)$, $\text{tr}(\cdot)$, and $(\cdot)^{-1}$ denote the determinant, trace, and inverse of a matrix, respectively. Since parameters in delay and angular domains are assumed to be independent of each other, they are estimated separately to reduce the complexity.

To solve the ML problem, an initial solution is first provided and it significantly impacts the algorithm's convergence efficiency. For delay parameters, identifying the base delay associated with each DMC process is important. By observing the measured delay PSD, we can find that there exist multiple independent DMC processes. To detect the transition points in the slope of each process, the first-order difference technique is applied, thereby determining the dataset of each DMC process with different data lengths. Then, the initialization approach in [35] is adopted to estimate initial channel parameters of each dataset. Given that each DMC process spans a unique duration, it is crucial to normalize the base delays so that they

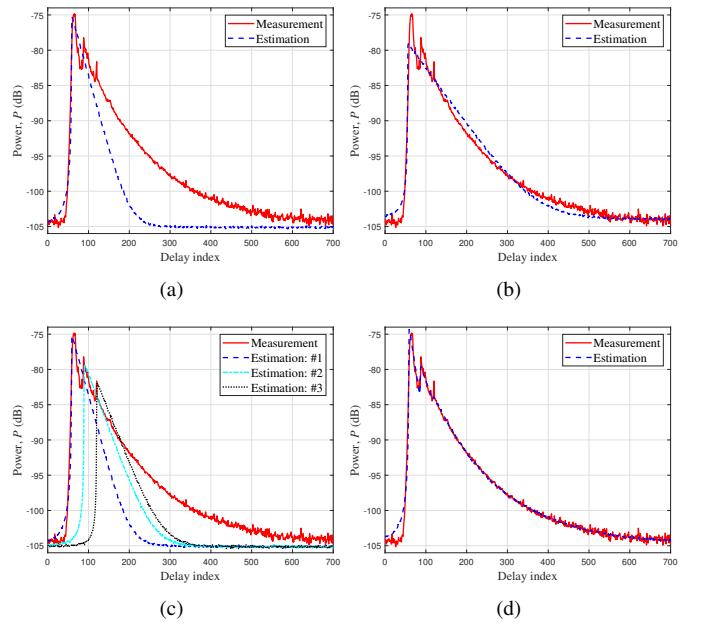


Fig. 3. Comparisons of (a) initial and (b) iterative estimation results for one DMC process as well as (c) initial and (d) iterative estimation results for three DMC processes.

can be computed under an equivalent number of frequency points. As for the angular parameters, an initial approximation is derived from the Bartlett spectrum. Subsequently, the Levenberg-Marquardt algorithm with gradient function and fisher information matrix is employed to get iterative results. Detailed calculations of these functions can be found in [35]. Using the estimated SMC and DMC parameters, the CIR can be synthetically reconstructed and compared to the measurement result. Firstly, a matrix of zero-mean complex Gaussian distributed values $\mathbf{z} \in \mathbb{C}^{M_f \times M_R M_T}$ is introduced. Then, the Cholesky decomposition is performed to obtain the transform matrix \mathbf{L}_F with $\hat{\mathbf{R}}(\boldsymbol{\theta}_F) = \mathbf{L}_F \mathbf{L}_F^H$ in the delay-frequency domain and \mathbf{L}_A with $\hat{\mathbf{R}}(\boldsymbol{\theta}_A) = \mathbf{L}_A \mathbf{L}_A^H$ in the angular domain. Finally, transfer function matrices of the estimated DMCs and full channel can be obtained by

$$\hat{\mathbf{H}}_D(f; \boldsymbol{\Theta}_D) = \mathbf{L}_F \mathbf{z} \mathbf{L}_A \quad (10)$$

$$\hat{\mathbf{H}}(f) = \hat{\mathbf{H}}_S(f; \boldsymbol{\Theta}_S) + \hat{\mathbf{H}}_D(f; \boldsymbol{\Theta}_D). \quad (11)$$

Fig. 3 compares estimation and measurement results of a single DMC process and those of three DMC processes during both initialization and iteration phases. For a single DMC process, there is an obvious difference in power decay rates between the initial estimate and iterated solution, indicating the presence of at least two distinct slopes. The iterative result captures about 79% of the total power. In the proposed method, three independent DMC processes are modeled in the delay PSD. Fig. 3(c) shows the initialization results based on this assumption. After an iterative process with ten iterations, the estimated delay PSD aligns closely with the measurement data, capturing about 99.6% of the total power, thereby demonstrating a satisfactory match.

IV. MEASUREMENT RESULTS AND ANALYSIS

In this section, we present a comprehensive analysis of channel characteristics for SISO and MIMO channel measurements in IIoT scenarios. The obtained LSPs such as DS, KF, and ASs, play an important role in generating accurate SSF channel models. By illustrating the effects of DMCs on SVs and channel capacities, we highlight the critical importance of accurately incorporating DMC characteristics into IIoT channel models. Therefore, the comparative analysis of channel characteristics between SMCs and DMCs provide a basis for the development of DMC models.

A. SISO Measurement Results and Analysis: Delay PSD, PL, SF, ED, DS, KF, and Amplitude Distribution of SSF

1) *Delay PSD*: Fig. 4 displays the measured delay PSDs of positions Rx71 in Case 1 and Rx281 in Case 2, which are located at identical positions with different heights of Rx antennas. During channel measurements, the Tx antenna is at the right rear of the metal pillar and the link between the Tx and Rx is obstructed by the metal pillar. Hence, the LOS path is not dominant and they are considered as NLOS positions. The estimated MPCs, indicated by '*' in Fig. 4 are distinguished by applying a threshold. The threshold is determined by the larger value of 10 dB above the noise floor (Threshold1) and 20 dB below the maximum power (Threshold2). It is evident that a reflection path with stronger power exists in Case 2, thereby resulting in a higher threshold for determining MPCs in Case 2 compared to Case 1. This leads to the extraction of more MPCs in Case 1 and similar received power (denoted as Pr in Fig. 4) as in Case 2. Furthermore, the delay PSDs exhibit abundant MPCs and evident trailing in IIoT scenarios. For SISO channel measurements, it is difficult to distinguish SMCs and DMCs from the delay PSD without the angular information. Channel characteristics are analyzed based on the all extracted paths, thereby including SMCs and DMCs. Comparisons between SMCs and DMCs are demonstrated through MIMO channel measurements.

2) *PL and SF*: The PL helps to conduct the link budget, determine the numbers and locations of required APs, and assess the intra-network interference. There are two empirical PL models available for fitting measurement results, i.e., Close-In (CI) PL model and Floating Intercept (FI) PL model [14]. The equations of these models can be expressed by

$$PL = 32.4 + 20\log_{10}(f_c) + 10n\log_{10}(d) + X_\sigma \quad (12)$$

$$PL = \beta + 10n\log_{10}(d) + X_\sigma. \quad (13)$$

The center frequency and distance between Tx and Rx are denoted as f_c and d , respectively. The fitted parameters include the Path Loss Exponent (PLE) n , the intercept β in dB, and the SF X_σ assumed to follow a normal distribution with a mean of zero and a standard variance of σ in dB. If $n = 2$ in eq. 12, the PL of free space is obtained. To keep a fair comparison between the CI and FI models, the intercept of the CI model is designated by $32.4 + 20\log_{10}(f_c)$.

Fig. 5 demonstrates the PL of measurement and model results in Case 1, Case 2, and office environments. The PL

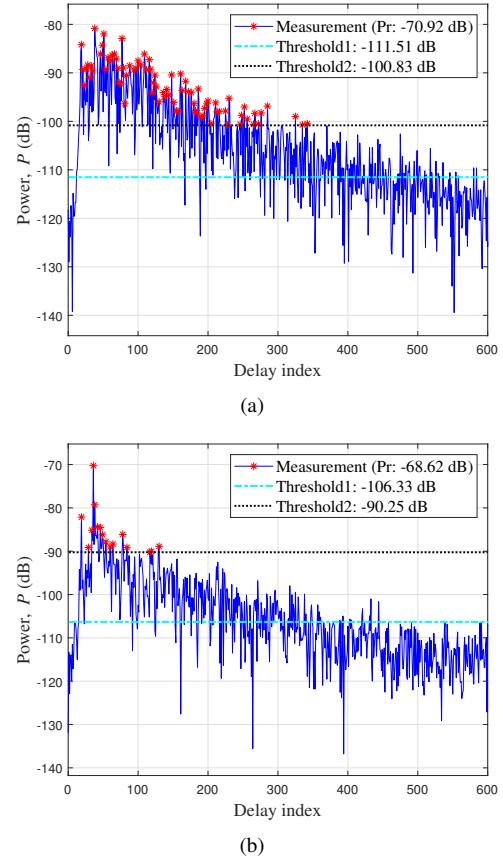


Fig. 4. Measured delay PSDs in IIoT scenarios at (a) position Rx71 of Case 1 and (b) position Rx281 of Case 2.

of IIoT scenarios is lower than those of the office scenario and free space. Due to the larger physical size and more metal objects in factory environments, there are rich scattering MPCs that can increase the received power. In IIoT scenarios, the PL results in Case 1 and Case 2 exhibit minimal disparity. In Case 1, the Rx antenna height is merely 0.3 m, which is significantly lower than most scatterers. Hence, the number of MPCs that satisfy the threshold is larger and the received power is high. In Case 2, there exists a higher probability of receiving wall reflection paths with strong power compared to that in Case 1. Consequently, there is negligible difference in PL between both cases. The PL of Case 2 in NLOS scenarios has two segments with the second segment being 5–10 dB higher than the first. This increase in PL is attributed to locations Rx340–368 where the height of Tx antenna is slightly lower than that of nearby scatterers on the operation island and the blockage loss is larger.

Parameters of the two fitted PL models and 3GPP TR 38.901 [37] (referred to as 3GPP in the subsequent context) model are summarized in Table III. Notably, the PLE values for IIoT scenarios are smaller than those of 3GPP model, which aligns with findings from [14], [17], [20], [25]. The difference between CI and FI models is slight in LOS scenarios but due to the presence of two segments in NLOS scenarios of Case 2, the parameters of FI model differ from those of the CI model. When excluding the data from the second segment, the three parameters (n, β, σ) for CI and FI models are (1.61,

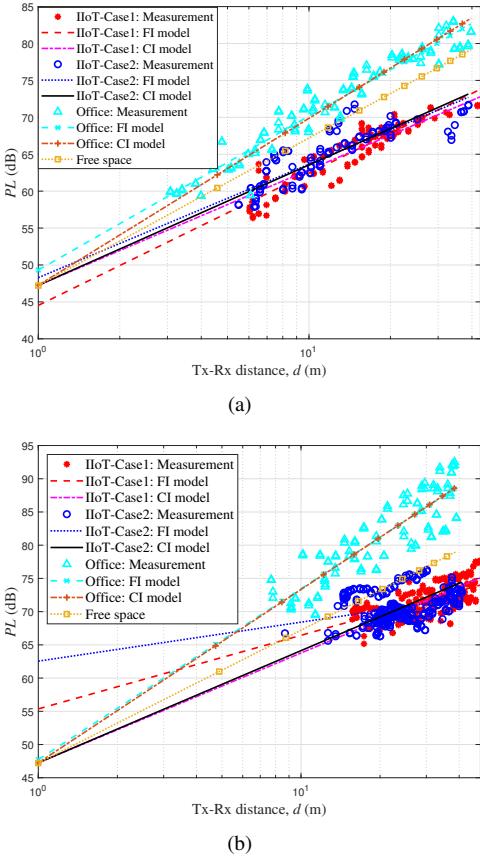


Fig. 5. PL of measurement, CI model, and FI model results for Case 1, Case 2, and office scenarios in (a) LOS scenarios and (b) NLOS scenarios.

TABLE III
PARAMETERS OF CI AND FI MODELS IN LOS AND NLOS SCENARIOS.

Cases		LOS scenario			NLOS scenario		
Parameters		CI model	FI model	3GPP model	CI model	FI model	3GPP model
IIoT-Case 1	n	1.56	1.79	2.15	1.65	1.11	3.57
	β	47.25	44.53	45.91	47.25	55.36	33.41
	σ	1.6	1.52	4	1.91	1.76	5.7
IIoT-Case 2	n	1.63	1.54	2.15	1.69	0.59	3.57
	β	47.25	48.28	45.91	47.25	62.55	33.41
	σ	2.12	2.11	4	2.63	2.23	5.7
Office	n	2.26	2.09	1.73	2.61	2.57	3.83
	β	47.25	49.31	47.25	47.25	47.71	47.25
	σ	1.85	1.76	3	3.13	3.13	8.03

47.25, 1.33) and (1.15, 53.7, 1.2), respectively.

3) *ED and DS*: ED and DS characterize the channel dispersion in the time domain. DS determines the guard interval length in orthogonal frequency-division multiplexing systems and tap lengths in equalizer designs when combating inter-symbol interference [8]. Among the MPCs that satisfy the threshold, ED refers to the delay difference between the last MPC and the first MPC, i.e., $ED = \tau_L - \tau_1$. The DS can be calculated as [38]

$$DS = \sqrt{\frac{\sum_{l=1}^L P_l \tau_l^2}{\sum_{l=1}^L P_l} - \left(\frac{\sum_{l=1}^L P_l \tau_l}{\sum_{l=1}^L P_l} \right)^2} \quad (14)$$

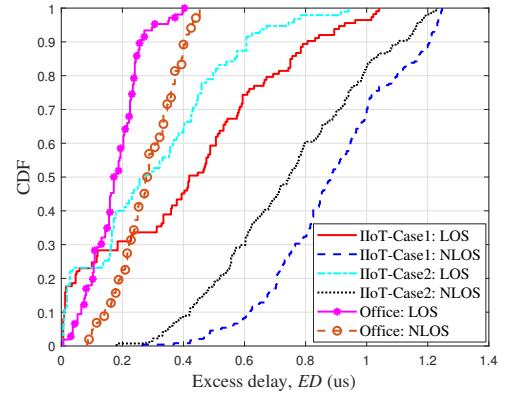


Fig. 6. CDFs of the measured ED in Case 1, Case 2, and office scenarios.

where τ_l and P_l are the delay and power of l th MPC, respectively.

Fig. 6 illustrates the Cumulative Distribution Functions (CDFs) of measured EDs in Case 1, Case 2, and office environments. It is evident that EDs are significantly lower in LOS scenarios compared to NLOS scenarios for both IIoT and office environments, due to the complex scattering environment in NLOS scenarios. Moreover, higher ED values are observed in Case 1 owing to the lower height of the receiving antenna and a larger number of MPCs. In addition, EDs in office environments are relatively smaller than those in IIoT scenarios where there are abundant metal objects. In [8], the size of the measurement area is $115 \times 28 \times 10$ m³ and the maximum 3D distance is about 118 m, larger than that in this work. Values of the ED for both LOS and NLOS scenarios were found to be 0.9–1.4 us and 0.4–1.7 us, respectively. Corresponding EDs in [30] were within the intervals of 0–140 ns and 0–200 ns for LOS and NLOS conditions, respectively. They are much smaller than results in [8] and this work since the maximum 3D distance is about 9 m. Therefore, larger measured 3D distance results in larger ED.

Fig. 7 presents the measurement and log-normal distribution fitting results of DS in Case 1, Case 2, and office environments, with the corresponding distribution parameters listed in Table IV. The DS and ED exhibit a similar trend because of analogous reasons. However, certain values may deviate from the expected distribution when Tx-Rx distance is small since the dominant LOS path can result in smaller DSs. Therefore, standard deviations in Case 1 and Case 2 are large. The DS in Case 1 is larger than that in Case 2 because of richer MPCs. Compared with results in the literature, distribution parameters of DSs are different because of different measurement configurations and environments. However, authors in [14] investigated the effect of antenna heights on DSs and revealed that a lower antenna height can result in larger DSs, which is consistent with our findings.

4) *KF*: The calculation of KF is consistent with the moment-based method in the frequency domain [39]. Fig. 8 presents the measurement and normal fitting results and distribution parameters are provided in Table IV. The KF in Case 1 is smaller than that in Case 2 due to the lower antenna height. Results in [15] also showed that higher antenna heights can

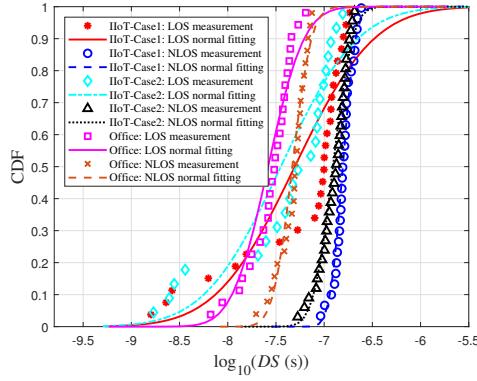


Fig. 7. DS of measurement and fitting results in Case 1, Case 2, and office scenarios.

TABLE IV
PARAMETERS OF DS AND KF IN LOS AND NLOS SCENARIOS.

Parameters	Scenarios	IIoT-Case 1	IIoT-Case 2	Office
$\mu_{lg}(DS(s))$	LOS	-7.41	-7.53	-7.58
	NLOS	-6.81	-6.91	-7.33
$\sigma_{lg}(DS(s))$	LOS	0.76	0.71	0.29
	NLOS	0.1	0.16	0.16
$\mu_{lg}(KF)$	LOS	2.12	3.44	0.57
	NLOS	-4.96	-3.66	-2.12
$\sigma_{lg}(KF)$	LOS	7.67	7.66	4.77
	NLOS	3.54	3.53	3.16

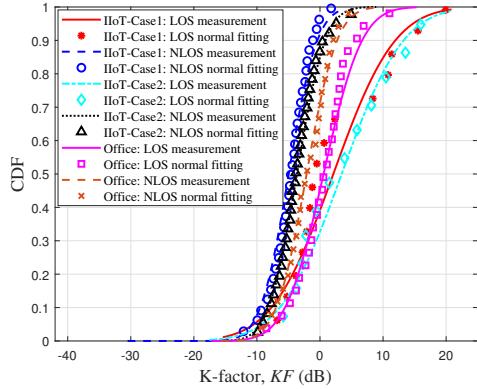


Fig. 8. KF of measurement and fitting results in Case 1, Case 2, and office scenarios.

decrease the probability of blockage and lead to a higher KF. In addition, the KF in IIoT scenarios is larger than that in office scenarios as some Rx positions are suited near to Tx without any obstructions between them. These positions have smaller DS and the strong LOS path leads to a higher KF.

5) *Amplitude Distribution of SSF*: There are 7 and 8 locally amplified positions in Case 1 and Case 2, respectively. The amplitude distribution of all frequency points for each amplified position is analyzed across 50 local positions. Fig. 9(a) is the amplitude distribution at position RxA1-5, fitted well by Rician distribution instead of Rayleigh distribution. The LOS path is dominant at this position and the KF calculated based on distribution parameters is 6.45 dB. In addition, the amplitude distribution of position RxA1-4 also follows a Rician distribution and its KF is 3.82 dB. Fig. 9(b) depict

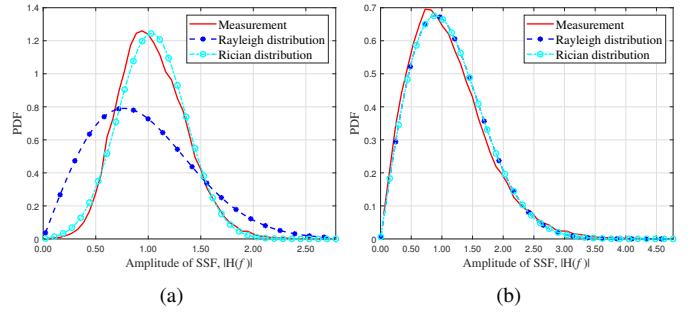


Fig. 9. Amplitude distribution of SSF for measurement and fitting results in IIoT scenarios at (a) position RxA1-5 and (b) position RxA2-1.

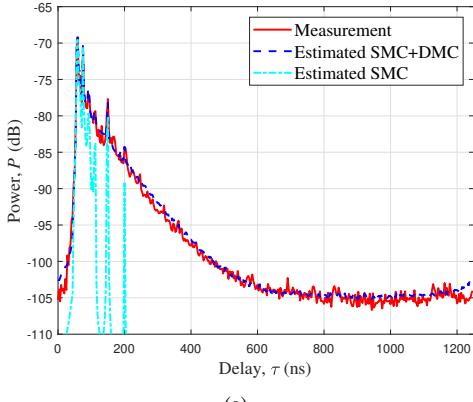
the well-fitted Rayleigh and Rician distributions at position RxA2-1. These two distributions coincide with each other due to a small KF of 0. Except positions RxA1-4 and RxA1-5, all other positions exhibit Rayleigh distributions in their amplitude distributions, consistent with results in [28] and [29].

B. MIMO Measurement Results and Analysis: Delay, Angular, Power, and Polarization Characteristics of SMCs and DMCs

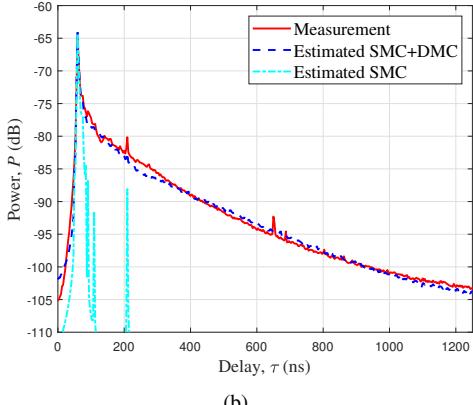
1) *Delay Characteristics*: In order to compare estimation results with only SMCs and those with SMCs and DMCs to measurement results, the delay PSD averaged over all polarized antennas under the LOS condition is illustrated in Fig. 10. Several strong SMCs with powers within 20 dB of the peak power exhibit obvious peaks in delay PSDs. These reflection paths and the LOS path can be well extracted by the SAGE algorithm and account for 59.59% and 44.91% of the measured power in office and IIoT scenarios, respectively. The Tx–Rx distances of these two positions are comparable, while the power fraction of SMCs in the IIoT scenario is smaller than that in the office scenario, indicating the rich scattering in IIoT scenarios. Additionally, measured delay PSDs exhibit obvious long trailing and are not entirely sparse within the delay domain, which is analogous to previous studies [8], [9], [20], [23], [32]. The trailing effect in IIoT scenarios exhibit a longer duration than that observed in office scenarios.

Considering the power proportion of SMCs and the shape of measured delay PSDs, it can be concluded that only SAGE algorithm is insufficient for extracting complete channel information. The channel is expected to comprise of both SMCs and DMCs. By combining estimation results of both SMCs and DMCs, the full average delay PSDs can closely match measurement results, which highlights the importance of the DMC modeling in the delay domain. Furthermore, the existence of DMCs may impede the detection of weaker SMCs [40]. This is due to that the SAGE estimator relies on the successive interference cancellation and every estimated path will be subtracted from the measurement data. When powers of SMCs are lower than those of DMCs, they will not be detected.

2) *Angular Characteristics*: Fig. 11 shows the joint angular PSD based on SAGE estimation results at position RxH22 in office scenarios [33] and position Rx11' in IIoT scenarios.

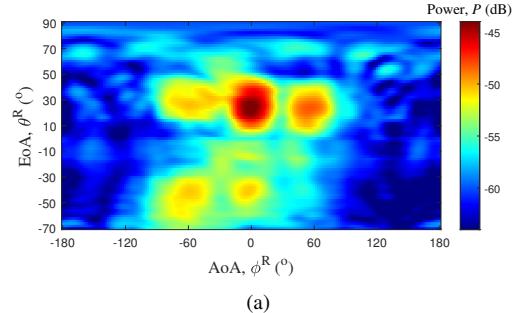


(a)

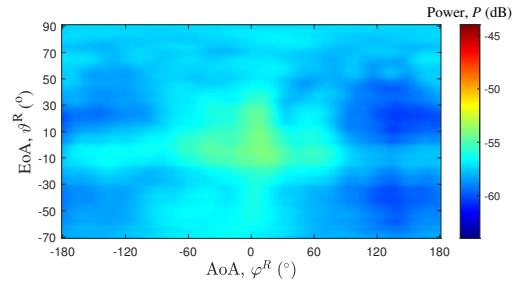


(b)

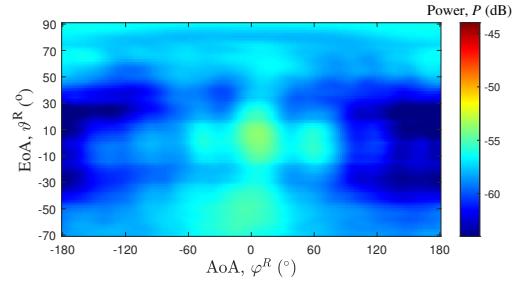
Fig. 10. Delay PSD of measurement and estimation results at (a) position RxH35 in office scenarios and (b) position Rx40' in IIoT scenarios.



(a)



(b)



(c)

Fig. 12. Angular PSD at position Rx82' in IIoT scenarios for results of (a) estimated SMCs, (b) measured DMCs, and (c) estimated DMCs.

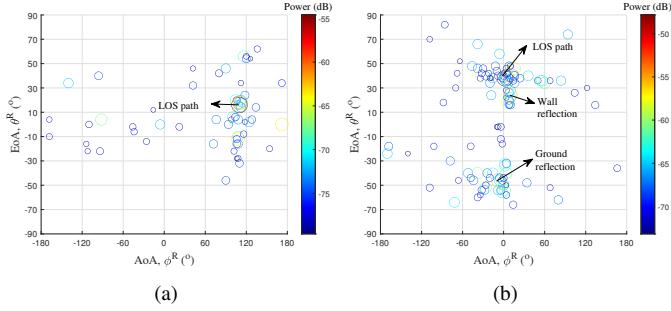


Fig. 11. Joint angular PSD of estimation results at (a) position RxH22 in office scenarios and (b) position Rx11' in IIoT scenarios.

Only MPCs whose power is within 20 dB of the power of the LOS path are used for analysis, and powers of MPCs with same angles are combined. In IIoT scenarios, there are a number of paths with EoA less than 0° and the ground reflection is very obvious. For office scenarios, MPCs are around the LOS path and the ESA is smaller.

Angles of DMCs cannot be extracted as individual paths like those of SMCs. Therefore, the Bartlett beamforming method is employed to investigate angular PSDs of DMCs. The dynamic range of Bartlett beamforming results is affected by the Signal-to-Noise Ratio (SNR) and the size of the antenna array. Higher SNR and larger antenna array can increase the dynamic range.

The Bartlett beamforming is calculated as

$$\mathbf{P}_B = \text{tr} \left((\mathbf{H}(\mathbf{f}) \mathbf{F}_{\text{T/R}}(\vartheta, \varphi)^H (\mathbf{F}_{\text{T/R}}(\vartheta, \varphi) \mathbf{F}_{\text{T/R}}(\vartheta, \varphi)^H)^{-1} \mathbf{F}_{\text{T/R}}(\vartheta, \varphi) \mathbf{H}(\mathbf{f})^H) \right) \quad (15)$$

where $\mathbf{H}(\mathbf{f}) \in \{\hat{\mathbf{H}}_S(\mathbf{f}; \Theta_S), \mathbf{H}_{D,\text{meas}}(\mathbf{f}), \hat{\mathbf{H}}_D(\mathbf{f}; \Theta_D)\}$. Assuming a uniform spatial covariance matrix across all frequency points, as stated by (8), the mean angular spectrum can be computed over M_f frequency points.

Fig. 12 illustrates angular PSDs of estimated SMCs, measured DMCs, and estimated DMCs at position Rx82' in the IIoT scenario. Here, measured DMCs are obtained by subtracting estimated SMCs from measurement results. For an obvious comparison of their angular PSDs, the maximum dynamic range in Fig. 12(a) is set for these three subfigures. It can be found that angles of SMCs are more concentrated than those of DMCs and powers of SMCs are larger. The assumption that the angular PSD of DMCs is uniformly distributed for both departure and arrival angles is not appropriate. The energy distribution of some DMC angles is centered around SMC angles, indicating the correlation between SMCs and DMCs. In addition, the estimation results by VMF distribution exhibit a good agreement with the measurement results.

TABLE V
PARAMETERS OF ASs IN LOS SCENARIOS.

ASs	Parameters	IIoT	3GPP Indoor Factory (InF)	Office	3GPP Indoor Hotspot (InH)
ASD ($^{\circ}$)	$\mu_{lg}(ASD)$	1.78	1.56	1.82	1.60
	$\sigma_{lg}(ASD)$	0.1	0.25	0.08	0.18
ASA ($^{\circ}$)	$\mu_{lg}(ASA)$	1.46	1.63	1.54	1.62
	$\sigma_{lg}(ASA)$	0.14	0.3	0.15	0.22
ESD ($^{\circ}$)	$\mu_{lg}(ESD)$	1.15	1.35	0.97	1.02
	$\sigma_{lg}(ESD)$	0.09	0.35	0.09	0.41
ESA ($^{\circ}$)	$\mu_{lg}(ESA)$	1.43	1.34	1.03	1.22
	$\sigma_{lg}(ESA)$	0.12	0.35	0.15	0.23

ASs describe the channel dispersion in the angular domain and can be calculated by the normalized angles [41]

$$AS = \sqrt{\frac{\sum_{l=1}^L P_l \bar{\phi}_l^2}{\sum_{l=1}^L P_l} - \left(\frac{\sum_{l=1}^L P_l \bar{\phi}_l}{\sum_{l=1}^L P_l} \right)^2} \quad (16)$$

and

$$\bar{\phi}_l = \text{angle} \left(\exp \left(j \left(\phi_l - \text{angle} \left(\sum_{l=1}^L \exp(j\phi_l) \cdot P_l \right) \right) \right) \right). \quad (17)$$

Here, ϕ_l can be four angles, $\bar{\phi}_l$ is the corresponding normalized angle, and $\text{angle}(\cdot)$ calculates the angle of a complex value. The logarithmic values of the four measured ASs are fitted by using the normal distribution, and their mean values $\mu_{lg}(AS(^{\circ}))$ and standard deviations $\sigma_{lg}(AS(^{\circ}))$ are presented in Table V. The ASD is greater than ASA in both IIoT and office scenarios, because the Tx is close to the wall and numerous metal objects surround the Tx antenna, causing signal divergence in all directions. The ESD is smaller than ESA as a result of downward radiation from the Tx antenna, limiting effective angle range to half of EoA. In IIoT scenarios, ESA exceeds that of office scenarios owing to diversified scatterer heights compared to close proximity between scatterer and antenna heights in office scenarios. The measurement results exhibit significant difference with those obtained by the 3GPP channel model [37], which may be attributed to differences in the measured environments and positions.

3) *Power Characteristics*: Fig. 13 illustrates the power fractions of DMCs in both IIoT and office scenarios [33] under LOS propagation conditions. The proportion of power occupied by DMCs in indoor scenarios is comparable to that of SMCs, ranging from 30% to 70%. It is consistently reported in [21]–[23] that DMCs contribute to a large ratio of the total power. Hence, the presence of DMCs cannot be disregarded in the measurement data. Furthermore, the power fraction of DMCs in office scenarios is slightly higher than that in IIoT scenarios. On one hand, the measured office environments also contain many scatterers and metal objects that can contribute to DMCs. On the other hand, the DMC power fraction is related with the Tx–Rx distance and the measured Rx positions are closer to the Tx position in IIoT scenarios compared to that in office scenarios, resulting in a lower DMC power fraction.

Fig. 14 shows the PL of measurement results, estimated SMCs, and measured DMCs in office and IIoT scenarios. To

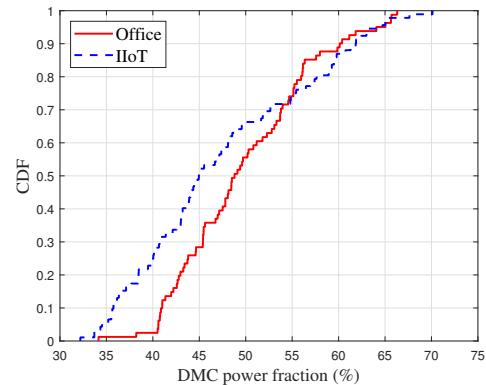
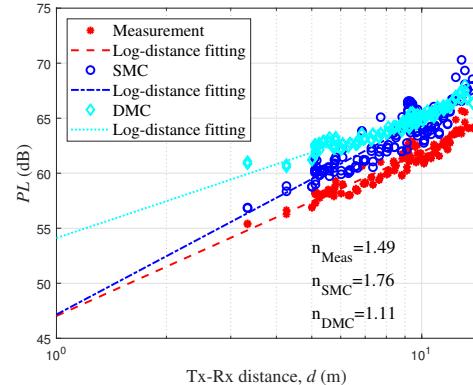
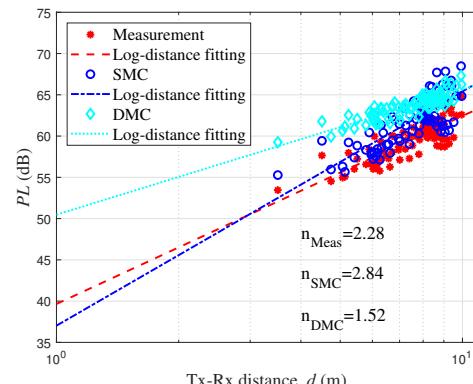


Fig. 13. The fraction of DMC powers in office and IIoT scenarios.



(a)



(b)

Fig. 14. PL of measurement results, estimated SMCs, and measured DMCs in (a) office scenarios and (b) IIoT scenarios.

determine MPCs from the averaged delay PSD, a threshold is set as 20 dB below the maximum power. Then, the total received power is calculated as the summation of path powers above the threshold. Different from the two-step model in [42], the PL is fitted only by the log-distance model. For both scenarios, the PLE of SMC results is larger while the PLE of DMC results is smaller than that of measurement results. Therefore, the power ratio of SMCs gets smaller and that of DMCs gets larger with the increase of the distance.

4) *Polarization Characteristics*: Fig. 15 is an illustration of the delay PSD for four polarization combinations in office and IIoT scenarios. For MPCs with small delays and strong

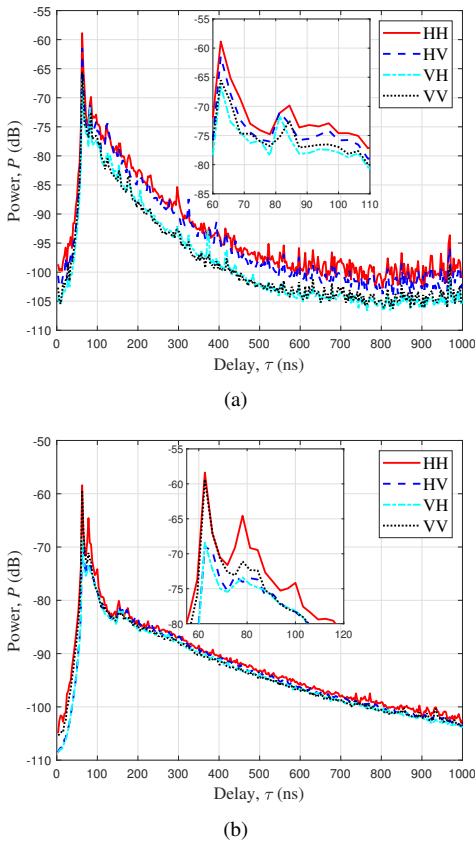


Fig. 15. Delay PSD of measurement results for four polarization combinations at (a) position RxH11 in office scenarios and (b) position Rx20' in IIoT scenarios.

powers, the received powers of co-polarized antennas are not necessarily higher than those of cross-polarized antennas since received powers of different polarized antennas are influenced by the relative position of Tx and Rx antennas. For MPCs with larger delays and weaker powers, the horizontal-polarized Rx antenna tends to receive more powers compared to its vertical-polarized counterpart regardless of the polarization state of Tx antennas. Given that the Tx antenna is horizontally oriented, it exhibits higher radiation efficiency in the horizontal polarization direction, thereby leading to a higher received power for the horizontal-polarized Rx antenna over the vertical-polarized one. Moreover, the IIoT scenario involves pronounced ground reflections, which can enhance the power received by vertical-polarized Rx antennas. Therefore, the difference in received powers of different polarized antennas will be reduced for MPCs with larger delays and weak powers in IIoT scenarios.

To investigate the statistical characteristics of the polarized received powers, XPRs for H and V polarizations as well as the Circular Polarization Ratio (CPR) are calculated as

$$\text{XPR}_H(\text{dB}) = 10 \log_{10} \left(\frac{\sum_p p_{HH}(\tau_p)}{\sum_p p_{HV}(\tau_p)} \right) \quad (18)$$

$$\text{XPR}_V(\text{dB}) = 10 \log_{10} \left(\frac{\sum_p p_{VV}(\tau_p)}{\sum_p p_{VH}(\tau_p)} \right) \quad (19)$$

TABLE VI
PARAMETERS OF XPR AND CPR BASED ON DELAY PSDS IN OFFICE AND IIoT SCENARIOS.

Components	XPR	Office		IIoT	
		μ	σ	μ	σ
Measurement	XPR_H	4.23	1.71	1.35	2.61
	XPR_V	-3.38	2.41	-0.3	3.22
	CPR	4.43	1.14	0.94	1.22
Estimated SMC	XPR_H	4.6	2.92	1.4	4.07
	XPR_V	-3.77	3.92	-0.42	4.53
	CPR	4.93	1.91	0.83	1.78
Measured DMC	XPR_H	3.44	0.39	1.29	0.63
	XPR_V	-2.91	0.72	-0.68	0.98
	CPR	3.87	0.47	1.25	0.46

$$\text{CPR}(\text{dB}) = 10 \log_{10} \left(\frac{\sum_p p_{HH}(\tau_p)}{\sum_p p_{VV}(\tau_p)} \right) \quad (20)$$

where $p_{HH}(\tau_p)$, $p_{HV}(\tau_p)$, $p_{VH}(\tau_p)$, and $p_{VV}(\tau_p)$ are delay PSDs of four polarization combinations. Table VI presents the normal fitting parameters for measurement results, estimated SMCs, and measured DMCs. In both scenarios, mean values of XPR_H and CPR are larger than 0 dB while mean values of XPR_V is smaller than 0 dB. It is evident that the received powers for horizontal-polarized antennas are higher than those for vertical-polarized antennas.

For the delay PSD, there are a lot of MPCs in each delay bin. The power at each delay bin is the fading result after multipath effects. Based on the dual-polarized SAGE algorithm, channel parameters of each path can be extracted. XPRs for H and V polarizations as well as the CPR are calculated as

$$\text{XPR}_H^l = 10 \log_{10} \left(\frac{|\alpha_l^{HH}|^2}{|\alpha_l^{VH}|^2} \right) \quad (21)$$

$$\text{XPR}_V^l = 10 \log_{10} \left(\frac{|\alpha_l^{VV}|^2}{|\alpha_l^{HV}|^2} \right) \quad (22)$$

$$\text{CPR}^l = 10 \log_{10} \left(\frac{|\alpha_l^{HH}|^2}{|\alpha_l^{VV}|^2} \right). \quad (23)$$

In LOS scenarios, XPRs are computed separately for the LOS path and NLOS paths. In the ideal condition, the LOS path has no polarization rotation and only co-polarized powers are received. Hence, the XPR would approach infinity. However, in channel measurements, cross-polarized powers of the LOS path can be received due to various non-ideal factors. Therefore, the XPR of the LOS path describes the maximum measurable depolarization extent due to these non-ideal effects [43]. Table VII summarizes the normal distribution parameters of XPR and CPR results for LOS and NLOS paths. For the LOS path, mean values of XPR_H and XPR_V are much larger than those for NLOS paths. The presence of numerous metal objects makes MPCs susceptible to polarization rotation. The XPR_H is larger in office scenarios while XPR_V is larger in IIoT scenarios, which are consistent results in Table VI. As mentioned before, the existence of ground reflections enhances the power received by the vertical-polarized antennas.

TABLE VII
PARAMETERS OF XPR AND CPR BASED ON ESTIMATED SMCs IN OFFICE AND IIoT SCENARIOS.

MPCs	XPR	Office		IIoT	
		μ	σ	μ	σ
LOS path	XPR _H	20.58	6.21	17.92	7.24
	XPR _V	13.08	5.75	15.74	7.43
	CPR	1.33	3.55	0.45	4.32
NLOS paths	XPR _H	7.89	9.85	4.3	9.11
	XPR _V	2.25	9.03	2.28	9.17
	CPR	3.49	8.62	0.71	8.71

C. Effects of DMCs on SV and Channel Capacity

1) *SV*: The SVs of a MIMO channel matrix indicate the number of parallel independent sub-channels available and determine the capacity of each data stream. The calculations are performed in the frequency domain with the normalization factor γ applied to all sub-channels in order to normalize the channel transfer function matrix, which is expressed by [44]

$$\mathbf{E} \left[\frac{1}{\gamma} \|\mathbf{H}(f)\|_F^2 \right] = M_T M_R \quad (24)$$

and

$$\bar{\mathbf{H}}(f) = \frac{\mathbf{H}(f)}{\sqrt{\gamma}}. \quad (25)$$

Here, $\mathbf{E} [\cdot]$ is the expectation operator and $\bar{\mathbf{H}}(f)$ is the normalized channel matrix. The SVs can be obtained through singular value decomposition at each frequency point

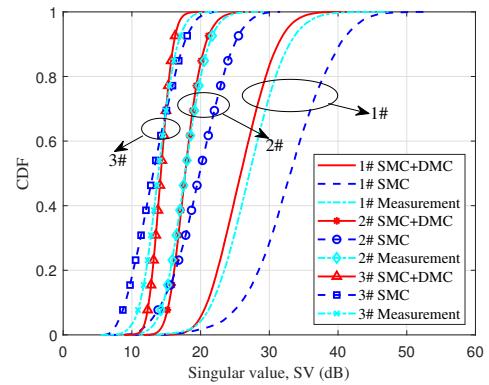
$$\bar{\mathbf{H}}(f) = \mathbf{U} \mathbf{D} \mathbf{V}^H. \quad (26)$$

In (26), $\mathbf{U} \in \mathbb{C}^{M_T \times M_T}$ and $\mathbf{V} \in \mathbb{C}^{M_R \times M_R}$ are unitary matrices, and $\mathbf{D} \in \mathbb{R}^{M_T \times M_R}$ is a diagonal matrix composed of all SVs. Fig. 16 illustrates the measurement and estimation results of the first three SVs in office [33] and IIoT scenarios, which account for 62.63% and 68.03% power of the channel matrix, respectively. It is evident that the disparity between the measurement results and estimations with only SMCs is greater than those with both SMCs and DMCs. This highlights once again the significance of DMCs.

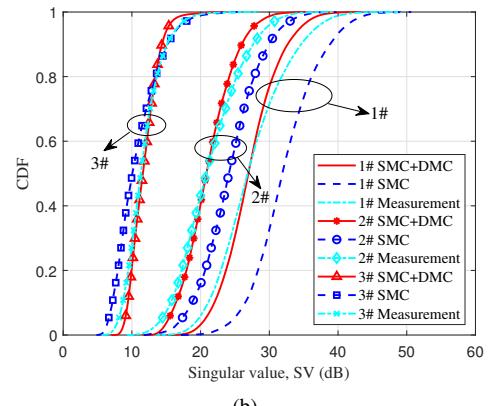
2) *Channel Capacity*: The channel capacity is calculated based on the normalized channel matrix $\bar{\mathbf{H}}(f)$

$$C = \mathbf{E} \left[\log_2 \left(\det \left| \mathbf{I}_{M_R} + \frac{\rho}{M_T} \bar{\mathbf{H}}(f) \bar{\mathbf{H}}(f)^H \right| \right) \right] \quad (27)$$

where ρ denotes the SNR, \mathbf{I}_{M_R} represents the identity matrix of the order M_R , and $\det |\cdot|$ calculates the determinant of a matrix. The channel capacity of measurement and estimation results in IIoT and office scenarios [33] under a SNR of 5 dB is illustrated in Fig. 17. Relative errors of estimation results with only SMCs are 36.79% and 39.82% in office and IIoT scenarios, respectively. However, relative errors of estimation results including both SMCs and DMCs in these two scenarios are 3.68% and 4.17%. Neglecting the DMCs will lead to an underestimation of the channel capacity.



(a)



(b)

Fig. 16. First three SVs of measurement and estimation results in (a) office scenarios and (b) IIoT scenarios.

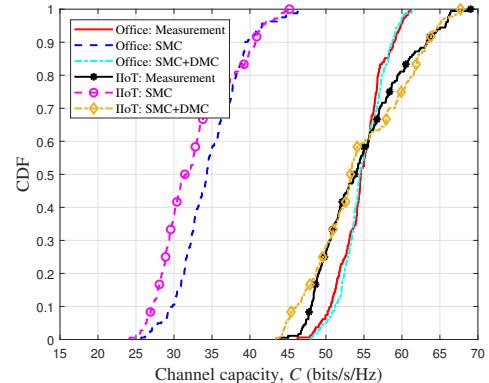


Fig. 17. Channel capacity of measurement and estimation results in office and IIoT scenarios.

V. CONCLUSIONS

This paper has conducted both SISO and polarized MIMO channel measurements at 5.5 GHz with a bandwidth of 320 MHz in IIoT scenarios. Two typical communication scenarios, i.e., APs and industrial terminals installed on AGVs as well as those distributed across the manufacturing area, have been explored. For SISO channel measurements, various channel characteristics including the delay PSD, PL, SF, DS, ED, KF, and amplitude distribution of SSF have been investigated. Results have shown the PL in IIoT scenarios is comparatively smaller than those observed in office scenarios and free space,

while the difference between PL results of Case 1 and Case 2 in IIoT scenarios is small. Besides, both DS and ED for Case 1 and Case 2 have been found to be larger in IIoT scenarios as compared to those obtained from office scenarios. Results have shown that DS and ED are larger while KF is smaller in Case 1 due to the lower antenna height compared to Case 2. In terms of MIMO channel measurements, delay, angular, power, and polarization characteristics of SMCs and DMCs have been analyzed and compared. The average delay PSD has shown multiple DMC processes in IIoT scenarios, and therefore the estimation algorithm for multiple DMC processes has been proposed based on the algorithm for a single DMC process. Angular PSDs in IIoT scenarios have been found to exhibit an obvious ground reflection. Besides, results in both scenarios have shown the existence of DMCs and the power fraction of DMCs accounts for 30% to 70%. In addition, the polarization status has pronounced effects on the received power and the horizontal-polarized Rx antennas tend to receive more power. Finally, the effect of DMCs on SVs and channel capacities have been explored. Results have shown that ignoring DMCs can overestimate SVs and underestimate channel capacities.

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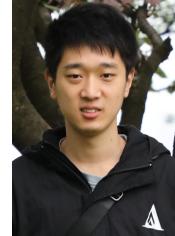
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