**A. Overview**

The following provides some of the thinking in the pcb design. The design intends to provide a number of hardware configuration options. Some of these are to facilitate testing and program development and would not be needed in a later refined design. Provisions have been in a number of places for implementing some circuit using alternate parts that have differing footprints.

This bms connects to a 16 series cell battery module. Multiple battery modules (e.g. six or seven) are connected in series to make a battery string. Hence, a battery string would use six or seven of these bms boards. The boards communicate and get their power via a CAN bus cable. This CAN bus cable carries the two CAN signals, plus “system” ground and system 12v (nominal), plus a signal line for a master reset. In addition to the modules on the CAN bus there will be a CAN node that is the “energy management controller” (EMC), though some other node might provide the EMC functions for the early implementations.

Since the battery string floats, or is lightly biased via very large resistors, all of the battery modules are isolated from the system ground. The bms board processor and bms ic ground is at battery module minus level. CAN, FAN control, master reset, dc-dc power, are all isolated from system ground. More detail on this later.

This board can accommodate a STM32F405RxT6, STM32F446RxT6, or STM32L431RxT6 processors. These are all 64 pin LPFQ packages. There small differences in the power pins so there is provision of the pcb for zero ohm or capacitors in several locations. The main target processor is the ‘L431. This processor has comparator and op-amp features not available in the ‘F405 or ‘F446, and is somewhat lower power as well.

The BMS controller is the Texas Instruments BQ76952, in a 48 pin LPFQ package.

The main features of the bms are--

- Low current module charger (approximately 80 ma)

- Cell-by-cell voltage measurement

- Cell-by-cell discharging

- Thermistors (three on BQ adc, plus two on processor adc)

- FET to discharge entire module via a resistor

- FET to turn on module heater

- FAN controller

- Headers for external pcb for external (to BQ) FET discharging

- Header for I2C

- Header for two external processor controlled LEDs

- Header for SWD (ST’s Single Wire Debugger, non-isolated!)

- Header for UART (non-isolated!)

The files for this project are on github repository--

https://github.com/GliderWinchItems/BMS

The files of interest for the board design described here, within the repository, can be found at

hw/eagle/bmsbmsBQ/bmsbq.sch and ‘.brd.

The general board layout has three ground plane sections. The leftmost (as viewed in eagle .brd) is the system ground (and 12v, etc.). The middle section is processor ground (which is at battery module minus level) and the right section the BQ76952 bms wiring (which is also at battery module minus level). The processor ground and BQ ground are connected at one point to reduce the effect of digital noise from the processor with the BQ adc measurements.

**Note:** The eagle file was renumbered with the prefix “100” for parts on the underside layer.

**B. CAN bus cable connections**

A 10 pin ribbon with IDC type plug plugs into the bms board with a 2x5 keyed header. At the other end it is crimped into a 9-pin female D connector and a short distance onward to a male D connector. These 9 pin D connectors are mounted on the battery module box. Cables daisy-chain the battery modules together. Having the chain form a ring allows cutting the current drop in the power carrying wires in half. To reduce voltage drop the plus and minus wires are tripled.

1 – system +12V

2 – system ground

3 – CAN L2

4 – CAN H2

5 – system ground

6 – master reset

7 - system +12V

8 - system +12V

9 - system ground

10 - unused

**12v polarity protection--**

Reverse polarity protection is provide by a pfet (FET103). The FET blocks if the +12v and system ground are reversed.

**Input current measurement--**

A thru-hole 0.1 ohm series resistor (R5) allows for measuring the current input.

**Master reset--**

The master reset line is used to reset the processors on the CAN nodes, i.e. reboot. This might be used to reset for program re-loading over CAN, simply restart during development.

The master reset master reset to a H11L1S opto-coupler (OPT101). Pulling this line to system ground turns on the coupler and pulls the NRST (reset) line on the processor to ground. The 3.3K, R121 resistor on the opto input limits the current on the input, and the 10K, R8, pull-up resistor holds the NRST line normally high. The pushbutton allows manually resetting the processor. Diode D5 on the opto input protects against reverse polarity.

**LED-12V power--**

LED2, 6.8K, R18 indicates that 12V power is present.

**CAN 5v supply--**

From the 12v power, the AP7380Y (REG1) linear regulator supplies 5v to the system side of the isolated CAN driver (ISO1042). The eagle net designation 5V/2. C121, 4.7u, and C108, 4.7u, provide the necessary input/output capacitors.

**FAN 12v supply--**

Given the cooling fan(s) are 12v +/- 10%, but the system 12v will at times be 13.8v or even higher, a regulator is provided to limit the voltage to the FAN(s). There are two options. One is the LDK320 (REG3A) which is a SOT-89 package, which has a low quiescent current, but may not be available. The other is the venerable LM7812T (REG3B) which is a TO-220 package, but has an 8 ma quiescent draw. The regulator uses C1, 1u for the output, and shares C3 (1u), C122 (4.7u) on the +12 protected line.

The regulated FAN 12 goes to a 4 pin header (JP5)--

1 – system ground

2 – FAN regulated +12v

3 – FAN tachometer

4 – FAN on/off/pwm

The fan on/off/pwm signal is zero for off; weak fan pull-up or 5v for full on; or pwm 0-5v. To assure the FAN does not run when the processor is off, or not controlling the i/o pin, a 74LVC1G14 inverter (P$1) with its input pulled up with the 10K R107 resistor holds the FAN off when the opt0-isolator (OPT100) is not active. The R107 pull-up to 5V/2, system ground 5 volt supply, is also needed for the open drain OPT100.

To control the FAN the processor pin PA5 drives a NFET (FET102). Pull down resistor R??? assures a floating PA5 does not energize the FAN. The opto input current is set by the 1.8K R105 resistor and 5V/1, 5 volt processor ground side supply.

**12v supply LED**

LED1 with 6.8K R2, indicates that +12v protected polarity is present.

**C. Power supply chain**

**DC-DC 12 to 15v converter**

The +12v from the CAN bus cable is isolated and stepped up to 15v from the +12v protected line. There are two converter options. PYBJ6-D12-S15 (IC1A) and AMG1215SNZ (IC1B). These produce a regulated 15v output with an input voltage in the 9-18v range. They are rated at 6W. The PYJ6 will sustain the 15v to about 1.4 the rating, which at 15v is about 560 ma. The output voltage regulation holds up to the cutoff limit then drops rapidly, i.e. a sharp knee.

The 15v supplies the power to the processor ground domain. The battery module trickle charger is the main consumption of the power. Stepping up the 12v input to 15v helps with the charger switching to boost to the module voltage which will be 16 times the cell maximum voltage, ~56 (LiFe) or ~67v (LiPo).

**5 volt processor (5V1)**

AP7380Y (REG100), with C111, 4.7u, and C123, 4.7u, supply 5v for the processor side--

CAN driver

FAN tach OPT1

74HC00 (IC1) FET drive logic

I2C bus pull-ups

Note: This supply could be eliminated if the I2C used external pull-ups to an external 5v supply, and the dump and heater FETs were chosen with gate thresholds low enough to work with the 3.3v processor.

**Vcc (3.3v)**

Vcc supplies the processor. Two regulator options are provided. If the processor is run at a low sysclk rate the linear regulator, AP7380Y, (REG1), is the most efficient. For larger currents, a TO200 footprint is provided that will handle a VOX7803-500 switcher, or LM7803v3. Input/output caps: C119 4.7u, C120 100n and C124 4.7u. The values might vary depending on the regulator chosen.

The input to the Vcc regulator is via a diode OR which allows powering the processor from several sources. One source is the 15v described above, via diode D1.

Another, via D2, is from the BQ REG2 output. The BQ76952 has provision for two regulators, fed from an external NPN transistor follower. The BQ registers allow setting the regulators to 1.8, 3.3, 5.0v. Using the 5.0v setting is convenient for the diode OR to the Vcc regulator input. The program controls whether the BQ REG2 is on/off as well as the voltage selection.

The third input to the OR, via D3, is from a P/N FET switch directly to cell #3 of the battery module. Cell #3 provides a voltage that is less than the 15v dc-dc converter so if the P/N switch is on and the CAN bus 12v is present the drain on the battery is limited to FET leakage.

FET1, and FET104 form the P/N switch. NFET, FET1, pulls down the gate of the PFET to turn it on. An external switch via JP1 can also turn on the PFET. Processor pin, PC13, can turn on the NFET. Resistors R4, and R125 assure the FETs are off when the external power is off.

A number of powering scenarios can be implemented with this arrangement. Being able to discharge the battery module to a voltage for long-term storage might require operating the bms without power from the CAN bus. In this case the processor must be powered from the battery module.

Vcc powers the following--

Processor

Two leds (internal plus external)

Two spare thermistor 10K pull-ups

NRST 10K pull-up

Vdd (analog voltage) is connected to Vcc via a bead and by-passed with C105 (0.1u) to reduce Vcc digital noise.

**VBAT**

VBAT supplies the RTC (Real Time Clock) domain in the processors. When Vcc is off, VBAT will maintain the RTC and associated sram registers. The RTC domain provides a means for saving a few values when the processor is in shutdown mode (where everything but the RTC is turned off).

It requires a mininum of 1.7v and draws less than 1 ua with the 32 Khz clock running. There are two alternatives for powering VBAT. One is with the BQ76952 regulator REG1. This can be set to 1.8v. A zero ohm resistor, R12, connects REG1 to the VBAT processor pin1 and C118.

An alternative is to install the MCP1810 linear regulator (REG101). This is a low quiescent current regulator powered from battery cell #1. The current drain, though continuous on the cell, is less than 1 ua so the unbalancing that cell from the others is negligible. R123 and C118 give some protection for hot-pluging the battery module to the board. R123 and the MCP1810 would not be installed if the BQ (REG1) method is used for VBAT.

Note that VBAT is internally powered from Vcc when Vcc exceeds the VBAT pin voltage.

**D. Charger**  
  
A low current charger boosts the 15v dc-dc isolated converter to the voltage of the battery module by switching with a FET. The FET turns on and the inductor current increases. The FET turns off and the inductor “flyback” dumps the energy into the battery pack. The strategy is to set a pwm rate and on/off ratio such that the current drops to zero during FET off time, and the current build-up during the on time results in delivering the power available from the dc-dc converter; usually called a discontinuous mode.

If the parameters are such that the current does not drop back to zero during the FET off time the current level increases each cycle and unless there is some mechanism for limiting the peak current eventually the something fails. If the build up is slow enough the dc-dc converter will eventually shutdown in overload mode. If the build-up is fast the output capacitance of the dc-dc converter may be sufficient to destroy the FET before the overload limit begins lowering the voltage.

Drive to the charger is from processor PA8, timer TIM1CH1. This drives the MCP1416 (or MCP1401) FET gate driver (IC102). The gate drive is supplied with 15v from the dc-dc converter. In addition to the output capacitance on the dc-dc converter module, pads are provided for C113, C114, C115, (4.7u, 0.1u, 10n). R118 is a small series resistor between the driver and FET gate, shown as 6.8 ohms on the schematic. It is expected that values of around 15 ohms might be optimum, but the FET and other factors will be involved. A test point, TP1, provides convenient access to monitoring the FET gate.

The size and type of inductor for the charger will be selected after some experimenting. The Coilcraft RFB1010 series, 47 uH, is expected to be a reasonable mid-point for the inductance. The pcb footprint is arranged with alternate hole spacings for various size thru-hole inductors and rectangular areas without solder mask for various smd mounting inductors.

The PMV280ENEA switching fet (FET3) was chosen for its small output capacitance and the 1.1a current rating is sufficient. The SI2324A has a larger output capacitance and somewhat higher current rating. The output capacitance factors into ringing when the FET turns off, and the period of the ringing can affect the current at the beginning of the next fet on duration.

The switch fet drain and inductor connect to diode (U$3) that reverse biases during the FET on duration and directs the energy to the battery when the FET turns off.

Several features are present to deal with the open circuit situation. If the voltage of the inductor/FET-drain is not limited in some manner, when the FET turns off there is nothing to limit the voltage and the FET will have to absorb the energy in the avalanche mode. To prevent FET damage a capacitor and scheme to detect an over-voltage, and/or zener to limit the voltage is available.

In the open circuit situation, capacitor C5 (thru-hole) or C112 (smd), [1u@100v](mailto:1u@100v), will start at 15v, and with each pwm cycle of the FET increase the voltage. When the voltage reaches the zener voltage the zener will limit further increases. There is a thru-hole and smd alternative for the zeners (D4 and D6). 82V is the expected value.

Since the charger can generate close to 5.5W of power and the zeners are rated at 0.5W or less, a means of detecting the over-voltage and turning off the pwm is needed. Several methods are possible.

One method of shutting down the pwm is to measure the voltage at the capacitor/zener junction. R115 and R119 form a voltage divider for input to the processor. Several variations are possible. One is to use a high value resistors that draw very little current from the output, e.g. 4M|210K. The divider impedance is too large for the processor ADC; 50K is about the amount where variable leakages begin to affect the ADC readings. Provision to deal with this is the inclusion of an op-amp follower, a TLV521 (IC101). The op-amp output feeds PA1 for the ADC measurement. However, for the L431, PA1 can be configured as comparator (inp) input with the other comparator internally connected to a DAC. The output of the comparator internally can activate the break input to timer TIM1 and immediately stop turn off the FET. If the comparator is not used, the program must rely upon the ADC measurement and turn off the FET. This of course is not immediate and until the software detects the over-voltage and turns off the FET the zener must dissipate the power. The comparator scheme is hardware and not software dependent, and in fact, it might be possible to eliminate the zener.

Another variation is a second output diode, PMEG10020 (U$100). This isolates the battery module from the voltage divider. With the voltage divider isolated the divider is no longer a continuous drain on the battery module. Smaller resistors can be used for the R115|R119 voltage divider and the op-amp follower eliminated, e.g. 64K|3.3K.

For FET current monitoring a 0.1 ohm resistor, R6, is placed in the FET (FET3) source. Test point, TP1, provides a place for a ‘scope. The voltage across the 0.1 ohm sense resistor is connected to PA3. In the L431 this pin can be configured for a comparator, and the other input to the comparator an internal DAC. The output of the comparator can be routed to timer TIM1 and turn the FET drive off when the current exceeds the DAC setting. This scheme is a hardware means for preventing the FET current from exceeding its rating.

The output of the sense resistor is passed through a RC filter for average current monitoring: R7 C6, 1.5K, 0.1u. For the L431, PA0 can be connect to the RC output via zero ohm R9. PA0 can be configured for OPAMP use and the output internally connected to ADC-IN8. For the F405 or F446 one has to be content with PA0 configured for ADC input.

For software control of the charging there are a number of strategies that can be employed. Using the L431 processor and comparators gives the most flexibility, as well as providing protection of the fet during software development.

Header JP3, R120 (1 ohm) provides a test point for measuring output current.

Test points--

TP2 – PA0 COMP1\_OUT

TP3 – PA2 COMP2\_OUT

TP4 – PA3 FET CURRENT SENSE

TP5 – PA6 TIM1\_BKIN\_COMP2

TP6 – PA11 TIM1\_BKIN2\_COMP1

**E. BMS**

**F. Misc**

**Dump**

For discharging the entire battery module FET (FET100) can switch in a 10W resistor mounted on the board, or a resistor connected to the two pin header JP17. Thru-hole pads are positioned on the board so that a 10W resistor can be mounted on the bottom side of the board. The resistor is not shown on the schematic. For an off board resistor, the header pin connected to the fet drain is expected to be connected to the resistor, and the other end of the resistor to battery module plus. The header pin for the fet source would be connected to the battery module minus. The minus connection avoid the resistor current passing through the board traces and battery module ribbon cable. R101 holds the fet off. R102 makes the fet act as a source-follower if the external minus connection is missing.

To prevent inadvertently turning on the dump fet the processor must set one I/o pin high (PC10) and another pin (PC8) low. IC1 gates invert and AND, as well as increase the voltage from the 3.3v processor to 5v, for driving the dump FET. R18, 470K, assures the gate input does not drift high if the i/o pin is not configured for output.

**Heater**

At times it may be necessary to warm the battery module before the first luanch. A FET for switching on a high wattage resistance is provided. A TO-220 footprint for FET2 provides for a high current fet. The same logic as above for “Dump” is used. In this case PC12 high and PC11 low that enables the FET. Two spade terminals are provide beside the FET. The same as for “Dump” there is R124 and R126. R104 handles the inconfigured PC12 situation.

**Dump2**

This provision might be used for some external load, e.g. a relay. Board space allowed adding this jic. FET101 is driven by PC6. Two pin header JP16 connects to the fet drain and source. R103 and R100 provide the protection in the manner described above.

**Spare thermistors**

Header JP12 can be used to connect to thermistors. PC4 and PC5 can be configured for ADC.   
R10 and R13 are pull-ups to Vcc.

If T2S on the BQ76952 is used for control, one of these inputs would be needed of three thermistors are needed.

**HSE**

Provision is made for the High Speed External oscillator, i.e. xtal control. Xtal, Q100, loading capacitors, C107, C109 (15p), startup resistor R112, 1M. Processor pins PD0, PD1.

**LSE: 32 Khz oscillator**

A crystal (X101) provides for 32 Khz LSE (Low Speed External) oscillator implementation. R108, 18M resistor is for startup. C100, C101 (10p) are the xtal loading capacitors. Processor pins PC14, PC15.

In the processor shutdown mode the RTC internal 32 Khz osc is shut down. With the xtal it will run in the LSE mode. In the other current low power modes the RTC internal osc runs.

**Spark gap**

Since the battery module ground is isolated and floating with respect to the system ground, provision for limiting a voltage built up that might breakdown one of the isolation barriers (dc-dc converter transformer, opto-isolators, or CAN driver). A pcb spark gap is made and labelled pad PD1. R3 can be a resistor for limiting sparkover current or fusing in more catastrophic situations.

**SPI/I2C pads**

Space allowed placement of four thru-hole pads (PD4-PD7) for connecting to SPI, or a second I2C.