

Study Notes for AWR Tutorial

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Abstract

These are study notes for the Advanced Writing and Research (AWR) tutorial.

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1 Introduction

This is an introductory tutorial to use AWR from the Roland device.

2 Videos

2.1 Design Troubleshooting for Stability Part 1

Instability arises from the use of feedback and gain together. This can be controlled by adding loss or adjusting bypassing in the lab to stabilize the circuit.

From AWR DE Tutorial 5

- After selecting the new schematic, name it and then press **Ctrl + L** to add elements.
- To see the details of a component, right-click and select **Help. [?]**
- You can add equations as in QUCS and use the factors in the component details.
- To tune an item or a factor on the graph, click the **Tune** tool above and then click on the factor; it will change to a blue color.
- Set the limit of the chosen factor and then click the tuner. It is behind the identifier tool that chose the factor to tune. You will see the variable tuner has limits and then you can change it above and below.

- To plot the output voltage (V_{out}), you need a voltmeter. Connect it in shunt with the load resistor R chosen from the element menu.
- To measure the DC characteristics of the amplifier (V_{out} vs V_{in}), you need a linear graph. Add a new measurement, select **Nonlinear** and then **Voltage**. Choose V_{DC} on the measurement component and place the voltmeter on the vertical axis. For the x-axis, use the voltage from the source.
- Click **Apply** and then choose the simulation tool on the schematic.

From AWR DE Tutorial 6

- From the elements menu, you can also find the voltage source (V source). If it is AC, to measure it you will need a voltmeter similar to the one used on the load resistor.
- The working frequency is a global value defined for the overall project from the project options menu. Define the frequency range and then from the global units icon above, choose the frequency and change its unit to kHz in this case.
- The netlist file that can be imported into AWR has the extension **.cir**. From the netlist menu, select **Netlists** and then choose **Import Netlist**.
- With **Ctrl + K**, you can add the important netlist.
- After adding the symbols, you can change them from square and normal device shapes from **Properties > Symbols**, then choose the needed shape.
- To add the voltage source, add **DCVS** and **ACVS** from the elements.

From AWR DE Tutorial 7

- The models that can be used in AWR are the PSpice models with **.cir** extension.
- These are called AWR netlist files.
- From **Steer 03.Wideband Amplifier Design Using the Negative Image Model, Part F**, we can see that the model used with the transistor is added in the data files above the graphs.

From Impedance Matching AWR

- From project options, you can change many of the item units.
- You can use the cookbook for ADS and check the LNA simulation part and try to replicate it in AWR.
- To measure the input impedance, it is a linear measure, and you can find it on the graph after adding a new measure. Choose Z_{in} .
- Define Z_{in} unit, the port number, and the source name. If there is a transmission line after the input port, it will appear.
- It is important to sweep the frequency and define the number of points for measurement to determine at which frequencies the device should read a measurement. This can be done from the project options window.
- To add another plot on the graph, click **Duplicate Measurement** and then from the window called **Modify Measurement**, you can add the changes between the two lines.
- For the 50-ohm resistor, if you change the Z_{in} measure from 75 ohms with the transmission line to 50 ohms, you will see matching at 50 ohms for Z_{in} real and the imaginary value is zero, indicating matching.
- In the case of 75 ohms with a 50-ohm transmission line, you will see the imaginary part increase with frequency from -20 to +20. If the imaginary part is greater than 0, it means positive reactance, indicating inductance, and negative reactance means it is capacitive.

- If you remove the resistor and use just the transmission line and simulate, you will see the real and imaginary parts are 0 ohms at 2.4 GHz if the transmission line is open, not grounded. If grounded, there will be a very large Z_{in} at 2.4 GHz.
- In the matching case, measure the impedance on the Smith chart and check where the point is for your frequency. Connect a series capacitor and a parallel inductor if the point on the Smith chart is on the capacitive part under the middle line. Then tune the values of C and L and check which one has a larger effect on the point. Tune it to get the point above on the inductive part, then with the capacitor value change it to reach the middle line indicating the point is totally matched.
- After adding a microstrip line with T-line used as a load, it should be matched when the length and the width give a 50-ohm for the material used on the substrate. In this case, the microstrip line and the T-line are 50-ohm, meaning they should be matched around the frequency of the T-line, which is 2.4 GHz. Matching can be seen from the impedance linear graph or from the Smith chart.
- If you have just one port, you will measure on Smith just S_{11} . When measuring, it is a must to use the MSUB on the schematic to define the substrate for the transmission line. The values of the variables on the MSUB are taken from the window where we define the width and the length on the MSline, meaning ϵ_r and $\tan \delta$ and so on.
- When matching with MSline, define the length and then you can add a parallel one in front of the MSline and define the length and tune it to get the matched point. Adding the admittance might help on Smith to get a line to move with it. On the new line, you can play with the width and the length.
- The microstrip TEE or MTEE is used to connect the MS lines instead of connecting them together, which might lead to parasitic capacitance. So the idea is to make the design and see the Smith chart and match with the MS lines, and then control the length and width of the MS lines to get the matched point. Then connect them with the MTEE with a dollar sign which will connect the three sides with the equivalent width for the line.
- If an MS line is not grounded, you need to connect the Mopen line, which is an MS line with open termination.
- To see the length of the MS lines, you can see the layout graph and then import the other component models that define the layout. AWR requires some experience because it does not always have the best documentation.

Microstrip Antenna AWR Lab Video

- This video is important for working with T-lines.

3 Technical Note from the CEL Blog

The CE3512K2 is an air cavity package structure which is effective in reducing RF power loss consumed by the packaging material. For HEMT, the gate has high impedance at DC, so there is only a need for bias at the drain and connecting V_g directly. The bias at the drain is sufficient to use just the inductor, and it should be high enough to provide good RF isolation at the operating frequency. The inductor can also be part of the matching network. A shunt capacitor provides a low impedance point, creating a low pass filter for noise and unwanted signals from the DC source. As frequency increases, parasitic effects become dominant, necessitating transmission line-based components in both bias and matching circuits.

Transmission Line Matching The quarter wavelength ($\lambda/4$) transmission line is a crucial element in RF design. The ($\lambda/4$) can replace the inductor on rf isolation. and for this technique there is no frequency limit. Radial and rectangle open stub are the most common Tlines on rf. The coupling capacitors have undesirable effects as it has high insertion loss as a fraction of dB directly degrades the noise figure by the same amount and the matching network becomes complicated due to the parasitic effect of the high frequency capacitors.

output series capacitor has negligible impact on the circuit performance

you will need bias tee if you wanna exclude using the input capacitors to prevent dc coupling with the instrument during the measurement. this only on noise figure measurement.

Tlines component on the matching network usually used on the cas for the freq higher than 10Ghz

Ampleon is a good company for rf transistor with application note and references. as stated on the website edaboard.com after you have the transistor model you can chose a bias point then stability analysis with Rollet factor then design the input and output matching. also the power transistor has optimum load impedance that maximize the delivered power or the gain.

one simple measurement is to make representation for the S param and then compare between QUCS and AWR

for Simulation

add S2p on the data files by import then add it on the schematic as rectangle then click and from Properties change the symbol. then follow the circuit stubs as on the Matching with the AWR video. the bias circuit is to design the bias point and the matching to work on 50ohm on HEMT transistor has highrt breakdown voltage and high operational temp. $\Gamma(S) = \Gamma(opt)$ must be first for LNA connect the bias circuit and define the bias voltaged and calculate Rg and Rd and the capacitor and the inductors

4 From github (<https://github.com/aliruveycan/Maximum-Earnings-using-AWR-Microwave-Office-Amplifier-Design-and-Simulation.git>)

to simulate the transistor on the data files upload the s parameter file and on the graphs plot all S parameters graphs.

then you can match with the Tlines length as on the AWR 1 hour tutorial for Matching.

5 Diffrent pdf notes from google Image

From Ultra wid band amp by chengcheng Xu Rf amplifier is used to amplify small signal amplitude to a large amplitude in transmission and receive signal from antennas.

if the BW from 1.5 to 3.5 Ghz it means that the amplifier can be called 2 GHz amp so our amplifier can be called 1GHz or 800 MHz or 600MHz amplifier for the SNSPDs

Not understood phrase is the final gain is 20 dB with the power gain slightly below 30 dBm.

if the transistor IV curve is mostly linear then the output signal gain will be linear otherwise gain will be non linear.

Class A amplifier has poor efficiency when converting the dc power to high freq output power the lost power will br converted to heat on the device this power that is not converted to rf power but it provide great output to input linearity

Class B more efficient than A but it scarifies the output linearity to input signal ratio. lead to distortion on the output signal half of the signal only amplified

push pull configuration with two transistor may solve the class B amplifier issue.

if the spice model is not provided so the setup a bias network is not important you will use on the s2p file form the provider then you need to match the output of the transistor to the output matching circuit also consider the stability of the amplifier if it is conditional on unconditional stable.

the S22 matching with the output matching network is created first than the input matching network if S11 is not matched all the input power will not be deliver to the amplifier

the biasing circuit or bias point use one that is recommended from the the provider bias points means the points for the s2p files that provided Vds and Vgs and Id

chose the bias point that has gain near to your interested freq on the thesis they use s2p at 3v 60 mA bias this can be show from the graph for MSG/MAG and S21 dB you see that S21 has gain at the needed frequency.

this bias point also availble on the AWR software so no need to import the file on the Microwave office software

P1dB compression point is also important as the transistor it self is not linear so the output / input ratio can't be linear

it is defined as the point where the device output power and the linear model output different by 1dB.

this point where the device also start to provide Nonlinear behavior so you look at the p1dB point on the data sheet

if you wanna use another transistor you should follow the same process.

the FPD2250 has 1dB point 31dBm and if the gain is 10dB so the max power input to the transistor is 21dBm so you need to see the conversion of the power values to dBm and check the P1dB effect. the 21dBm will be above the output of the 1 st stage.

the stability is not related to which gain value of BW is the device it self is unstable this will not has an effect on what gain or other parameter so we need to use stable network to prevent oscillating output the stability on Microwave office is tested by K() and B1 parameter and also by SCIR1() and SCIR2() parameters of the device

K>1 and B not < 0

SCRR 1 will create solid line and dashed lines circles the inside or out side the l'solid line circle the solid circle will be the stable one. the goal is to be inside the stable region

Design steps

- add the transistor model and change it to symbol or leave it as it is.
- check also if it is available on AWR or not at the beaning
- design a bias point circuit should be stable or should be called stability circuit. there is no voltage sources as on fig on the tutorial just Rd and Rout and Rg and the two ports also you might need to use MSline and control its length tune the component then see the stability for K and B values.
- the above step is repeated for the two stages on their own.
- this stability test can be done on smith plot with the circles need to be studied alone.

Wideband Matching

- the goal is to have a Wideband at the first gain is not important at this point as the BW.
- so Gmax is not needed now check table one on the tutorial pdf
- matching method are Chebyshev matching and lumped elements matching
- Chebyshev matching is based on Chebyshev polynomial and the matching network is mostly consist of quarter wave transformer and from the BW and quarter wave transformer section number the impedance of each quarter wave transistor is generated Chebyshev Matching is on figure 12
- then you need to see the matching on smith see S11 and S22 it should be nearly perfect match means it is circled around the center point smith plot.
- as shown on figure 12 Chebyshev has 6 Tline for each S11 and S22 and the length of the quarter wave transistor need to be quarter of the signal wavelength. so the result now for RF application is not realistic and the design will be very large and amplifier detentions will be large
- so the Chebyshev matching is not implemented here.

Lumped element match

-

6 matching

on smith for any point to match it move with circle until you get a point on a circle that pass by the smith center which is 50 ohm matched.

on impedance smith series R go right toward the center line series C goes down series L goes up on the admittance plane the shunt R,L,C goes the same L up C down but R left.

on Lec 7 impedance match with smith video is very nice

if

$$z_o = 50\text{ohm} \text{ and } Z_s = 50\text{ohms} \text{ so } Z_i \text{ then normalized impedance is 1 means full matched}$$

Z_i which is represented on smith chart

adding resistor will add loss to your design so using L and C is enough and better. impedance match with the Tlines is very difficult compared to Lumped element but the idea is the same there is numerating on smith for the matching lines. but the middle line for the real is the same but the imaginary numbers are written now in terms of Λ .

Txline feature from AER Videos

from tools chose txline it is used to know how much width should the line be to be 50ohm or how length should be to 90 deg at 80 Ghz for example on the txline window change to mm on length and width using the arrow on the middle to change between the calcuation then use the length and width on the schematic then simulate to see the smith chart you will see the point is on the middle if smitt

Sweep feature on the parameter you want sweep click right then chose sweep define a start and end and steps. and define also by equation a value to initialize the variable. **Reflection coefficient measurement** from the graph and S11 measure but at the beginning you have to add measure port at the input all of that is on the polar plot not smith then tune the Tline length. and see the effect on S11

if you change the port to harmonic balance port you will be able to see the I V values on this device. time waveforms of I V. on elements it is called port1 you will see the wave source.after it you need a V meter or I meter from element chose V_{meter} and also I_{meter} I_{meter} on series after port and V_{meter} on shunt. from the graph rectangle on plot chose properties then measurement then chose which graph on left and which on right. side.

on the Tline is length 0 the I V time relation are on phase when change the length the VSWR is the same and the real part of the reflection coefficient is the same but the phase deg changes always this means the phase difference between IVtime relation will change.

due to the phase changes the Tline is considered as network from inductors series and capacitor parallel with the voltage source.

VSWR is the ration between

$$V_{max}$$

/

$$V_{min}$$

there are some simulation AWR videos on the Microwave labcast channel Simulation

- import the sparmeter and make graph for the device at the begining before anything.
- then you can make your graph from the graph tool
- first stabilize your circuit connet in out series R and shunt R at the out this will leads to unconditional stability.
- then you can check that by the K measure or SCIR1 ans SCIR2 for stability circle.
- now need to match over the wide band this is most important than getting gain. so BW is the important now
- the Match step is the most difficult this can be by the TLines and the lumped elements
- most popular on AWR the Tline method from the Txline tool you can characterize your Tline properties.
- Match output before the input it is easy and important for the gain means match s22 of the transistor with the output load or matching.
- then Match the input S11 for the transistor with the input circuit to be sure that the power will be deceived to the transistor otherwise it will not.
- now Design input match and output match seprately and check them on smith the trick here is to make the whore freq range around the match point middle of smith
- and define only the operating or project frequencies on fron Dc to 1 ghz and define for th txline frequencies the middle point 500 MHz or less it means to make the Wideband match you need to match around the middle frequency.
- after you make the matching circuits make blocks and connect them to the in and out of the transistor
- then check the gain now.
- then change the port to source nd simulate the power on the device to see the total power output on this case you will see only the part where the S parametr measured mean the linear region not the whole characterstcis this due to no Nonlinear model available for the transistor

- and due to no Nonlinear model the Nonlinearity mean P1dB and OPI3 points of the device will be read only from the datasheet as mentioned on the pdf tutorial by chengcheng zu. on the Tlines from the txline which is considered to be real Tline insted of the ideal one. you will use the stability T junctions when connect 3 Diffrent Txlines.

Matching Circuit Notes

- **From AWR Matching Tutorial**
- An ideal transmission line (Tline) is lossless and provides a perfect phase delay at a specific frequency, similar to what was discussed in class.
- Under the transmission lines menu, you will find the phase menu, where you can choose ‘Tlin’ and ‘Tloc’ options. These are used for the lossless case.
- For the Tline, Z_0 is the characteristic impedance. Keep it at 50Ω . EL is the electrical length, which is not the physical length, but the phase delay in degrees that will apply to the signal. F_0 is the center frequency, which is crucial for determining EL.
- To simulate the input impedance in ohms from the linear curves, choose ‘Zin’ and select only the magnitude. Then, generate your graph and measure from Port 1.
- The real part of Zin represents the resistance in ohms, while the imaginary part of Zin shows the reactance, which defines whether the circuit behaves capacitively or inductively (negative or positive reactance). This is where the matching process begins.
- If you measure the Zin for the Tline with only a ground connection, it will show a large value at the center frequency, indicating an open circuit due to the high impedance.
- If you want to control a frequency on the Smith chart, set it as the central frequency on the Tlines, observe its point on the Smith chart, and then move it up and down based on the admittance and impedance plots. Note that using resistors is not preferred, as they introduce losses.
- When starting to match with lumped elements, always begin with the L-network of an inductor (L) and a capacitor (C) together, then adjust it. Notice that increasing the capacitance lowers the impedance since $Z = \frac{j}{\omega C}$.
- After matching on the Zin Smith charts with a complex magnitude, you can create an S11 graph and observe the value at the matched frequency in dB.
- The problem with ideal Tlines is that they are not practical; they don’t account for losses, junction connections, or various parasitics.
- To work with real Tlines, you need a new schematic.
- Real Tlines rotate around the center point by a specific amount, unlike LC components.
- After defining the microstrip line (MSline) based on the Txline tool, prepare the substrate for your measurements using the same tool.
- To achieve matching, add series and parallel Tlines and adjust their length and width.
- Simulate a T-shaped Tline on the layout to check the design before fabrication. When connecting more than one Tline with a T-junction, ensure that the widths of the junction sides and the Tlines are consistent. Only change the length. The length should not exceed 20 mm to maintain the dimensions of the PCB after fabrication.
- The junction is called MTEE, and there is another variant called *MTEE\$*, which automatically adjusts the widths if you have different width Tlines.
- For the open-ended Tline, use ‘Mopen’ to terminate the Tline.
- There is a tool called ‘Snap Together’ on the toolbar. Just select all Tlines on the layout and press it, and everything will be connected automatically. The tool is located next to the ‘Tuner’ tool.

- If you want to solve everything in a 3D simulation, you will need an EM simulation, which is quite difficult.

from edaboard

- power transistor have optimum load impedance that maximize either the delivered power or the power gain
- if you connect the pspice model for the transistor you can use the IVVURVE tool to measure the graph for the transistor just connect the drain and the gate.
- also you could add the models for lumped elements like C or L and R you need to import the model on the net files. **tips**
- you can add series R at the gate to get stable device the output match is enough to use the output capacitor and the bias L_d , R_d with capacitor or without.
- also the gate the bias with L_g and series and parallel resistor.
- also the matching of the input is the most important mostly done with LC circuits
- as on the figure 2 series L and 2 parallel C with the coupling capacitor. note the capacitors are in front of the inductors.
- also the output match is done on the same way but it arranged this way series L parallel C and then repeated one time.
- on smith you measure S_{11} and S_{11}^*
- tuners helps a lot to find the points on smith.
- search about LTuner tool that shows smith chart as like boxing the matching circuit. it is connected after the ports directly means the capacitor are inside it.
- also on this circuit the inductor and the resistor are in series for the biasing.
- the port impedance must be conjugate of the optimum load or source impedance
- there are power matching and conjugate matching

optimization

- to begin optimization from view menu choose variable browser then mark on optimize for the variable you want.
- also there constrain option to define min and max values no need for it now
- after you mark to optimize choose the optimizer goal from the project list
- then choose the parameter you want control just S_{11} or S_{22} or any other measurement
- define the value at goal start option
- then define goal type $>$ or $<$ or $=$
- then define the bandwidth you want get this value on it on min and max options
- then you will find a mark on the graph you can move it on the graph and change the optimization goal by mouse
- repeat the process with other curves then see the other marker on the graph for the other optimizer goal .
- then in simulate menu click optimize
- on the menu choose Random local for the optimization method
- Max iteration means how many times the circuit simulated greater number better result but takes longer

Dc biasing at the end

- when you chose a s parameter file it has a Id and Vds values the bias Vdd is not Vds
- do use Rd which will give you the needed Id and use the Vdd to get the needed Vds
- using High Rg is nice to don't disturb the measurements for matching.
- use I meter and V meter to measure these values.
-

From Microwave Labcast Lecture 9
From Microwave Labcast Lecture 9

- Oscillating occurs due to Amplifier + Feedback. Some slides from the video are shown in figs. 1 and 2.

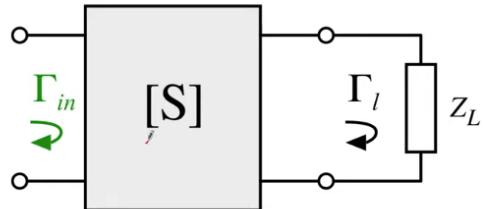
- Because Γ_{in} and Γ_{out} depend on source and load matching, the stability of the amplifier depends on Γ_S and Γ_L .

Thus, we define two types of stability:

- **Unconditional Stability:** if $|\Gamma_{in}| < 1$ and $|\Gamma_{out}| < 1$ for all passive source and load impedances(i.e. $|\Gamma_S| < 1$ and $|\Gamma_L| < 1$).
- **Conditional Stability:** if $|\Gamma_{in}| < 1$ and $|\Gamma_{out}| < 1$ only for a certain range of passive source and load impedances.

Figure 1: Stability Figure 1

Stability depends on the magnitude on Γ_{in}



$$\Gamma_{in} = S_{11} + \frac{S_{12}S_{21}\Gamma_L}{1 - S_{22}\Gamma_L},$$

Figure 2: Stability Figure 2

Stability

If the amplifier is to be unconditionally stable, Γ_S and Γ_L must satisfy the following conditions:

$$|\Gamma_{in}| = \left| S_{11} + \frac{S_{12}S_{21}\Gamma_L}{1 - S_{22}\Gamma_L} \right| < 1 \quad \rightarrow$$

$$|\Gamma_{out}| = \left| S_{22} + \frac{S_{12}S_{21}\Gamma_S}{1 - S_{11}\Gamma_S} \right| < 1$$

- The equations define a range for Γ_S and Γ_L where the amplifier is stable.
- This range can be found using the Smith charts and plotting the input and output *stability circles*.

Prof. S. Peik | Amplifier Design | 29 / 146 | CC BY

Figure 3: Stability Figure 3

Stability Unilateral Case

For a **unilateral** device, these conditions reduce to

$$|S_{11}| < 1$$

and

$$|S_{22}| < 1$$

that are sufficient for unconditional stability.

Figure 4: Stabilty for transistor and amplifier

- after the derivation for the Gamma in aout you get this for the C and R C is the center of complex numbers and R is the radius for the real numbers

Derivation of the output stability equation



Now complete the square by adding $|S_{22} - \Delta S_{11}^*|/(|S_{22}|^2 - |\Delta|^2)^2$ to both sides:

$$\left| \Gamma_L - \frac{(S_{22} - \Delta S_{11}^*)^*}{|S_{22}|^2 - |\Delta|^2} \right|^2 = \frac{|S_{11}|^2 - 1}{|S_{22}|^2 - |\Delta|^2} + \frac{|S_{22} - \Delta S_{11}^*|^2}{(|S_{22}|^2 - |\Delta|^2)^2}$$

$$\left| \Gamma_L - \frac{(S_{22} - \Delta S_{11}^*)^*}{|S_{22}|^2 - |\Delta|^2} \right| = \left| \frac{S_{12}S_{21}}{|S_{22}|^2 - |\Delta|^2} \right|$$

\Rightarrow In the complex Γ plane, an equation of the form

$$|\Gamma - C| = R$$

represents a circle where

- C is the center (complex number) and
- R is the radius (a real number).

Prof. S. Peik — Amplifier Design

Figure 5: Stability for transistor and amplifier

The equation defines the output stability circle with the center C_L and radius R_L where

$$C_L = \frac{(S_{22} - \Delta S_{11}^*)^*}{|S_{22}|^2 - |\Delta|^2} \quad (\text{center}), \quad (24)$$

$$R_L = \left| \frac{S_{12}S_{21}}{|S_{22}|^2 - |\Delta|^2} \right| \quad (\text{radius}), \quad (25)$$

Note that the procedure is the same as for the output, with interchanged S_{11} and S_{22} . Therefore we obtain similar results for the input stability circle:

$$C_S = \frac{(S_{11} - \Delta S_{22}^*)^*}{|S_{11}|^2 - |\Delta|^2} \quad (\text{center}), \quad (26)$$

$$R_S = \left| \frac{S_{12}S_{21}}{|S_{11}|^2 - |\Delta|^2} \right| \quad (\text{radius}), \quad (27)$$

Figure 6: Stability for transistor and amplifier

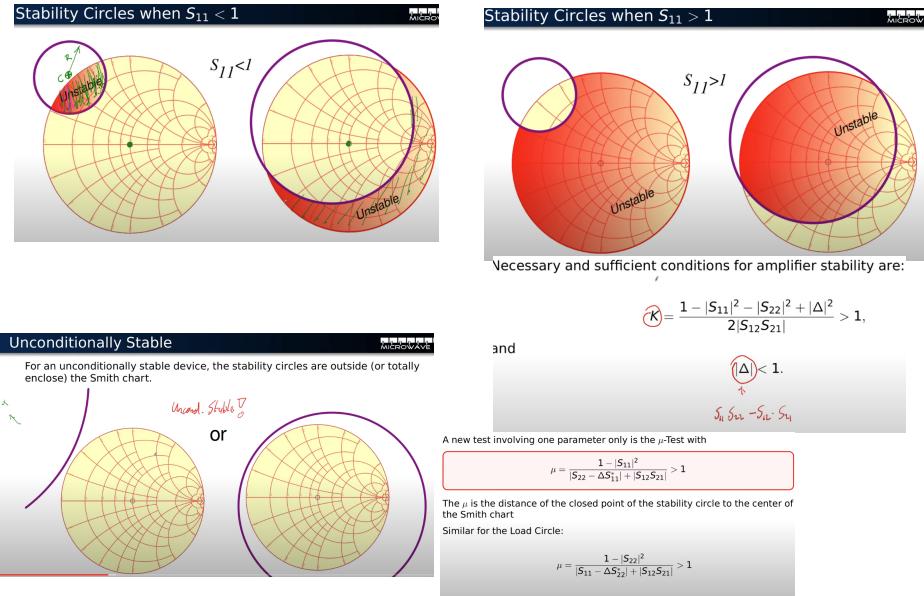


Figure 7: Stability for transistor and amplifier

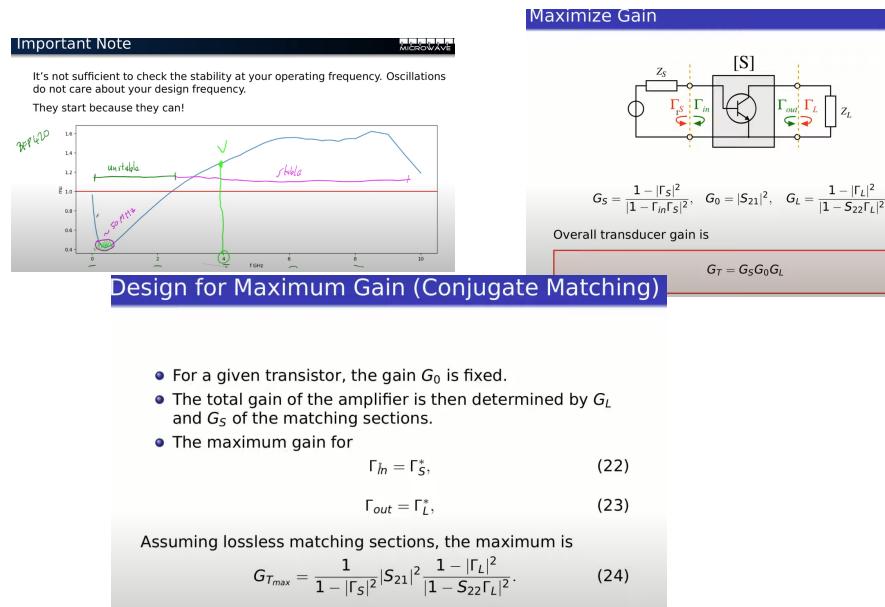


Figure 8: Stability for transistor and amplifier

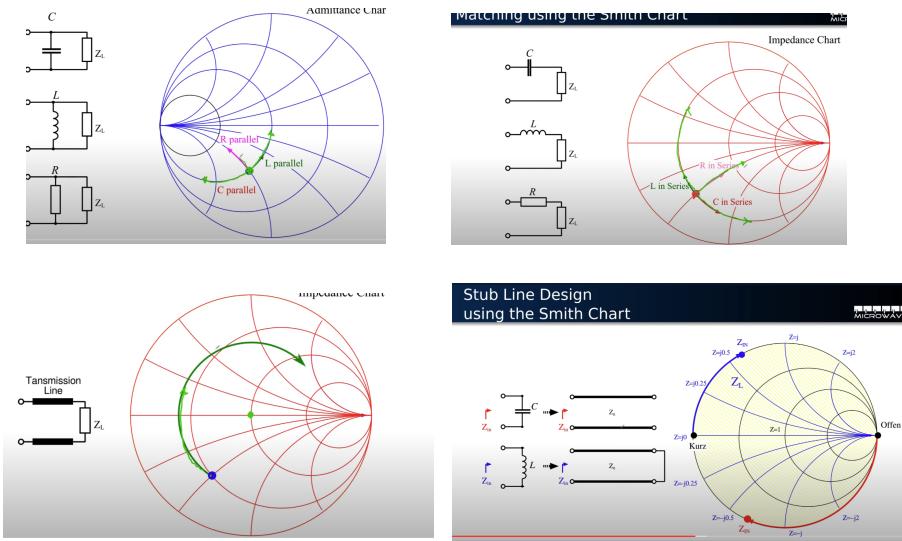


Figure 9: Stability for transistor and amplifier



Figure 10: Stability for transistor and amplifier

from sim videos

- this some pictures for some tricks used on the video during working with Tlines. as shown on fig fig. 11

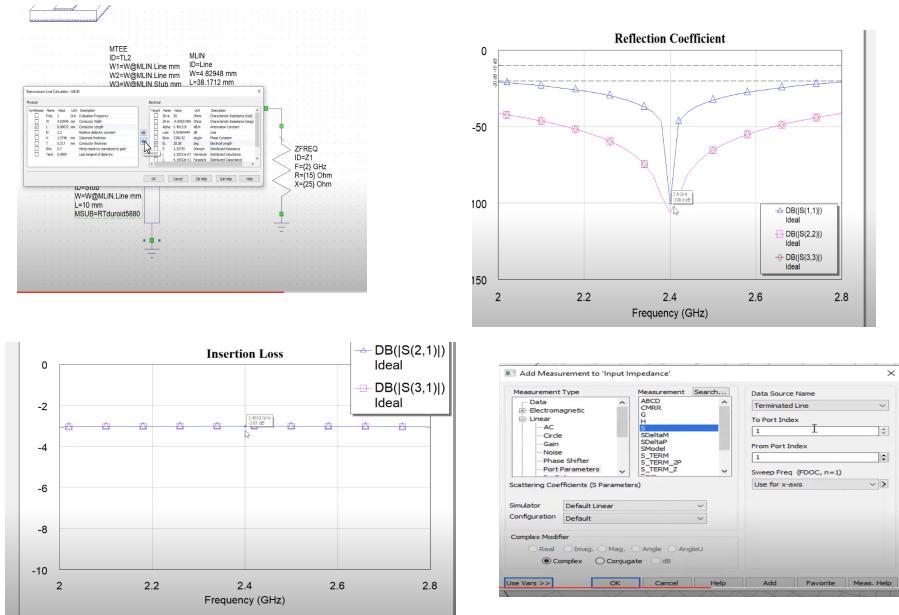


Figure 11: some tricks to write the tlines width and length also to use the tline calculator and update the line automatically also how to meaure the indertion loss and the the reflection coiffeent and also the input impedance

What to do to design

• stability ba K and delta or $SCIR_IJ(1, 2)$ and $SCIR_IJ(2, 1)$ on smith to be sure that all circles outside the smith means unconditional stability with the SCIR1 and SCIR2 for 22 and 11 should the spesified freq circle should be outside the the smith plot. all stability circles should be outside. the shunt resistor takes the circles outside to the open side right side of smith the series resistor takes the circles outside of smith from the left side or the short circuit side.

stability with MU1 ans MU2 and chose port 22 for the two values for the output stability A also this repeated with thr inputt match. don't chose a unit leave it normalised . MU > 1 for the stability with MU test. MU is the distance of the closed point of the stability circle to the center of the smith chart if MU < 1 the design will be potentialy Instability.

stability with $K>1$ and $\delta<1$ I think also the it works for 11 and 22 stabilize the design could reduce the gain also.

for the stability test add to the transistor inpur and output capacitors and the L shocks inductor on the line for the biasing circuit. then amke the stability test define the s parameter simulation from the points for the freq range for the transistor

like this circuit on fig. 12

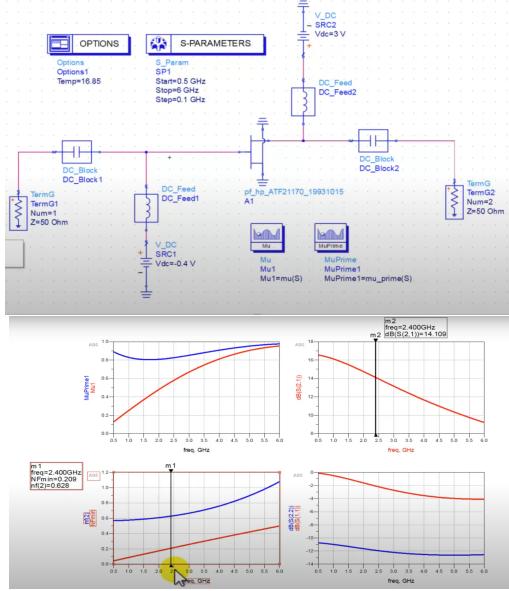


Figure 12: Stability for transistor and amplifier

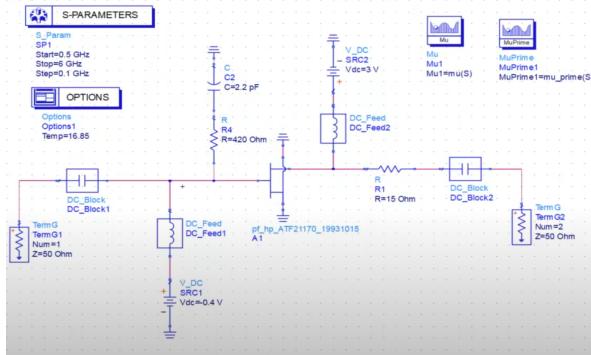


Figure 13: Stability for transistor and amplifier

so get the stability points vs the noise value. add series R at the in and out of the transistor directly like the R0 but use higher values.

avoid any noise components at the lna input which could lead to higher NF so the R0 for the stability could be at the output side only to avoid noise but the resistor the lower the better

adding the $V_{ds} = V_{dd}$ for the bias point for s2p file and also with V_{gs}

if the design is slightly stable or there value is lower than 1 by small value it could be solved during matching this is called potential stable but unconditional stability is preferred this for the unspecified freq range but for the BW it must be unconditional stable als using the feedback is good for the stability and the shunt RC line which is on input side this also can improve the stability but R shunt should be as high as possible for provide a load for the gate of the device the capacitor shunt is blocks the DC from going to the ground through the resistor with the stability in the dc bias line you can use the choke inductor for the low freq on the video it works for 2,4 Ghz so for our design it will also work otherwise

you can use the Mlines circuit and match it to be band pass filter means has very low S11 and S22 on the BW and zero S21 as a gain and this means no loss on the BW so make the circuit and match it by the way you are interested on it.

you can also use the capacitor on range pf beside the bias source as blocker and then use the choke inductor nad the resistor and make you measurement on the design. as mentioned on this graph for the biasing design also the connected radial stub gives double protection to the what happens on the capacitor besif the bias sourse it like a gnd point to protect the circuit. fig. 14

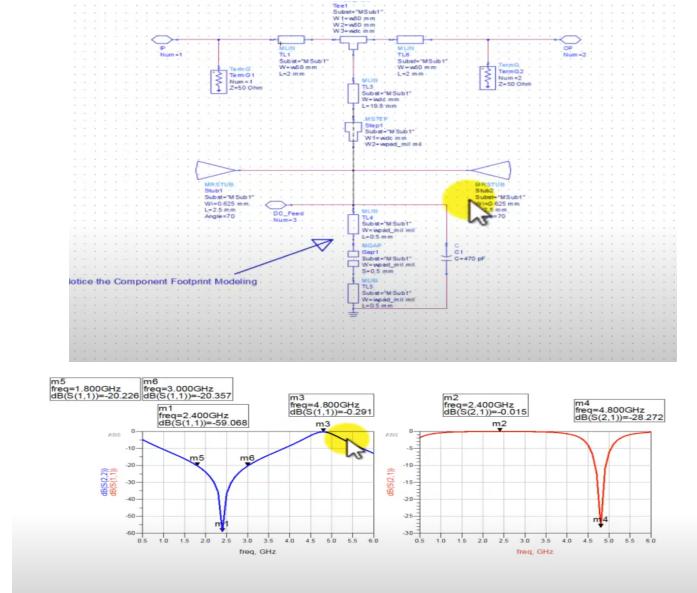
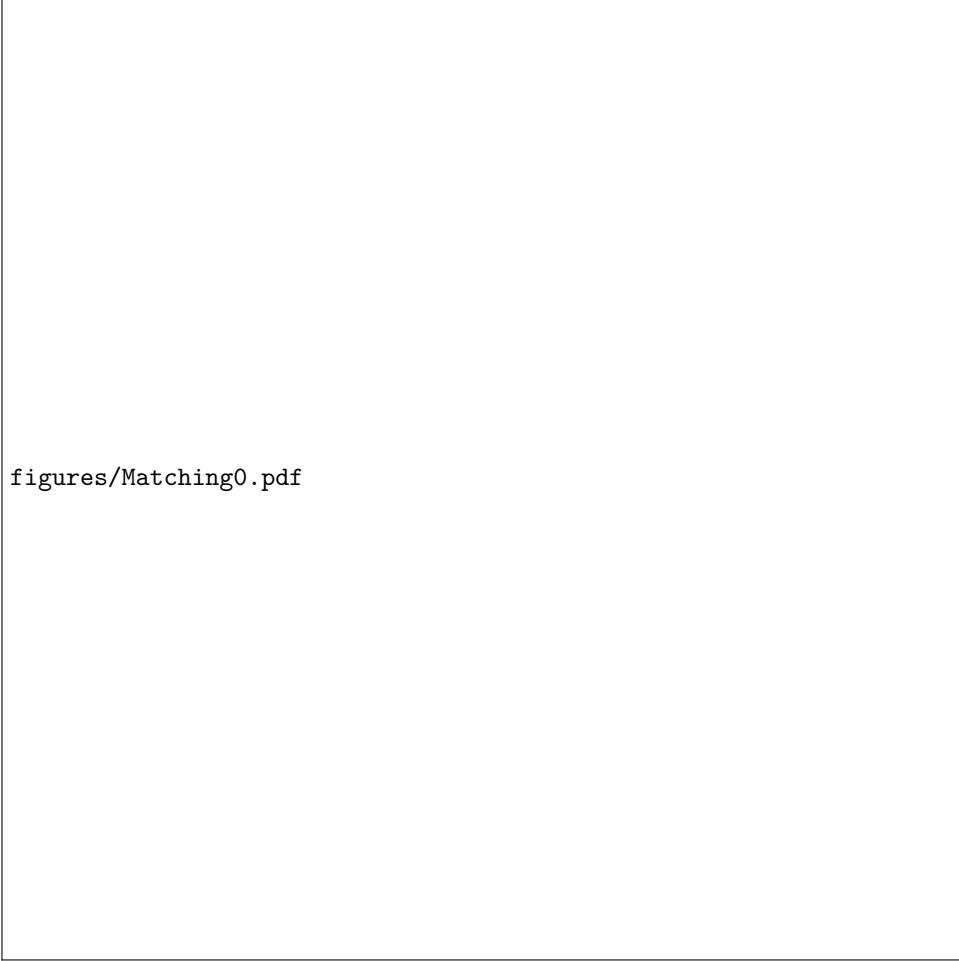


Figure 14: Stabilization for transistor and amplifier

on the optimization neever try to change the bias componet means the L chose stay as it is and the Rd just changet the component on the Rf propagation line.

for the matching at the end to get low S11 and S22 make the matching circuit and make the in and out capacitors par to it as you have to use them and shown the figure belloe fig. 15



figures/Matching0.pdf

Figure 15: Stabiliy for transistor and amplifier

also just change the compont realted to matching just the feedback and the capacitors and the shunt and series coponent on the propagation line this is an example for a matching circuits for the componet you are allowed to change.as in fig. 16

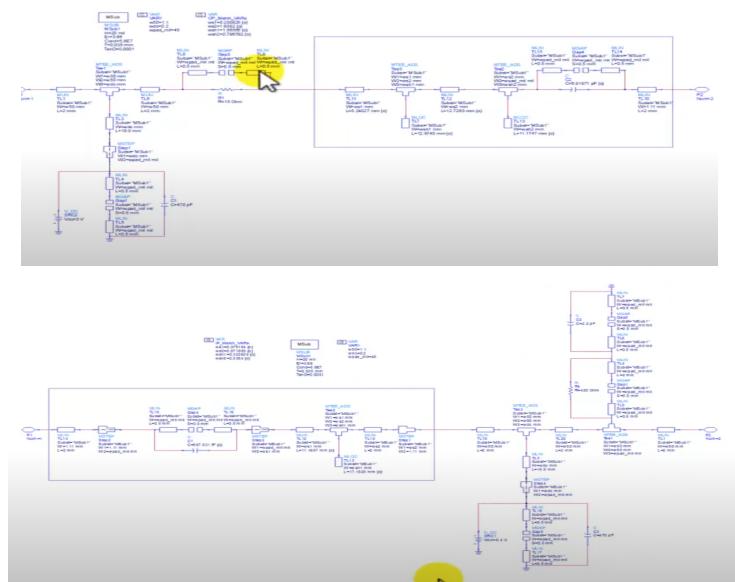


Figure 16: Stabiliy for transistor and amplifier

after every change make full measurement for the design all sparmeter measurement and the noise and the stability also the pdc is stable as you are using stable point for the biasing

the EM simulation for the layout can be done with s parameters model after you finish the simulation generate gerber file and fabricate you lna and during EM simulation the amp should be biased with the DC but on the S2p file it contains the value for the DC point.

for the p1db point if it should be higher than 10dbm for example. on the simulation for the Harmonic balance you sweep pin from -30dbm to 10dbm and measure the gain vs pin and see where is the 1db compression point. if it is in on 0dbm check the point also on vout(dBm) on this point and see if it oppose 14dbm for instance it means that our p1db point is on 14dbm and this means that our design achieve the goal to get $p1db > 10dbm$

this is on the RF design 10 by Anurag on youtube on min 50 .

for the noise figure from the steer video saved on Brave browser see the gain and Nf tuning graph see it and make it for your design. for the matching the stability is most important than it the stability controlled mostly by resistors at the input and the output also the feedback resistor

the biasing is interested on how much current on Id and the Vgs the mentioned Volt on the datasheet is the Vds and you just apply Vdd so you can control that with the feedback and the Rd you can use just inductors and the current will not change as it goes out from the source but with the Rd it might play role the stability and the biasing at the same time

using ID meter and the VD meter to measure the IV characteristic of the design make sure to use the marker on the graph that tells you the value of I and V at each point

the capacitors beside the biasing source is important for the biasing as it blocks the dc and force it to go to the design but it doesn't change the current across the voltage inside the circuit

now you can start match before checking the gain as matching over the specified BW is most important than getting the gain. so the blocking capacitors can be part of the match circuit

smith has a good notes as mentioned on this graph from Rf design 6 by Anurag fig. 17

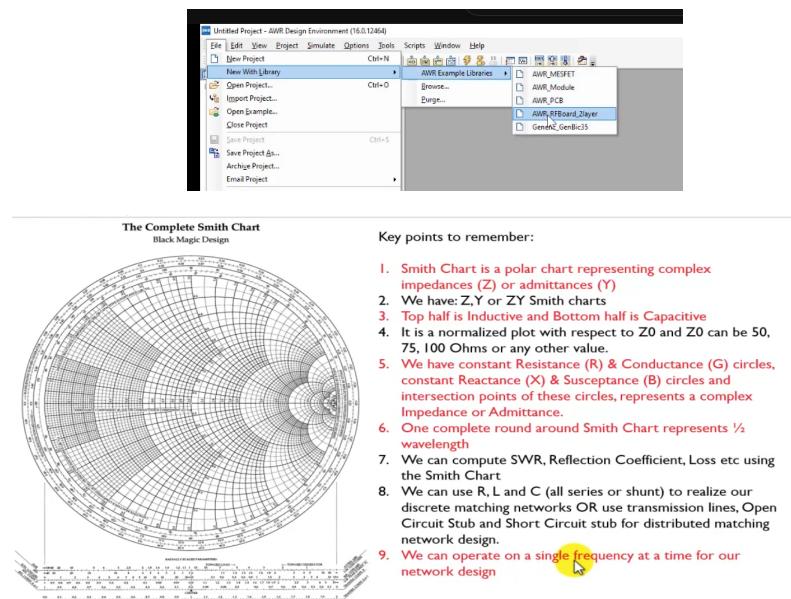


Figure 17: Smith important notes

you can make the matching circuit outside the blocking capacitors

start with measure the Z_{in} on smith for a specified freq as smith can work in single freq only check the in or the out impedance and match it with a 50ohm or any other source for example if the input of the transistor is 500 ohm and the source port is 50ohm now you will need to match Z_{in} can be considered S11 on complex units this might be a good idea for SNSPDs this for Z_{11} and Z_{22}

matching between two point is by finidng them in smith and then move one to the other point by the LC circuit this means that the interstage capacitor between the two stage LNA may be will no be enough for the matching between the two stages . for example if output of stage 1 is $10 + j * 50$ and the input of the 2nd stage is $50 + 100 * j$ so show the two poitns on smith and then move one to the other no need for 50 ohm matching here.

on matching you could add the two shunt or series beside each other but preferred to use one only. this point is important for our design due to the two component at the input amtch side if you don't wanna use a R and C . all matching network are simply filters between unequal termenation on each side

Broadband matching here we use the q circles method or called the $qfactor = centerfreq/BW$ then you will see a another graph at the middle of smith. as shown on fig. 18

Q factor is 1 if the you wotks on single freq higher q number means BW lesser and lesser and the circle increas the idea here is to make a smith inside the smith and you are only allowed to move only iside the smaller circle so every time you wanna change the directon you need a new component so the Match circuit will be many component not just an LC circuit as on the the graph fir 3 fig. 18

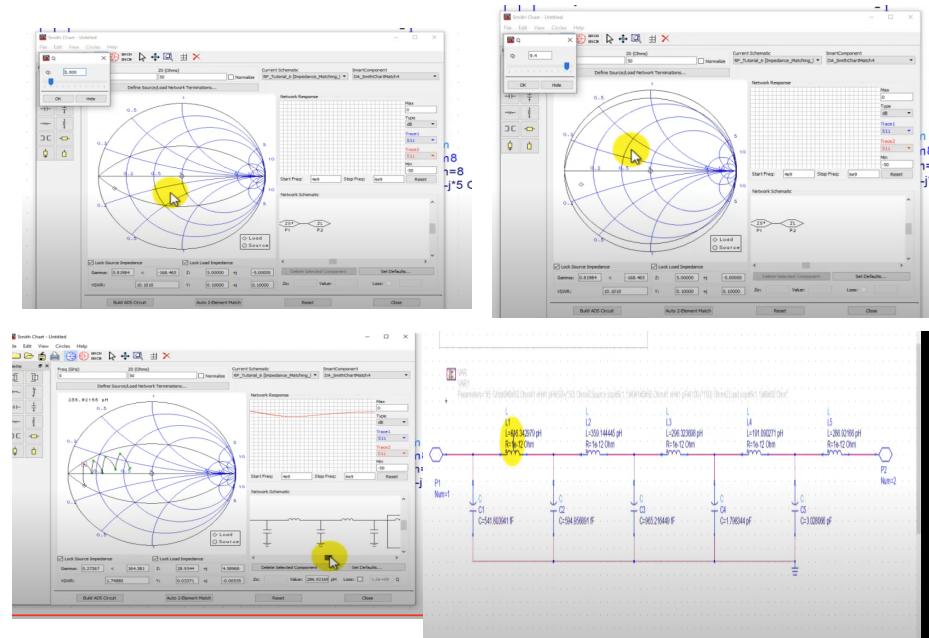


Figure 18: Smit important notes

but the whole circuit now is ideal component with 0 ohm resistance means q factor is very high more BW means More indertion loss or S21 and gain but the large amtching circuit is will add anoide figure on the LNA on the Power amplifr this might eat he output power if this is the output matching circuit. another point is the Broadband mactch will change the load and the source impedance during matching so this needs some tricks to deals with it.means the source and load impedance vary with the freq as you work on BW Impedance mactching importance fig. 19 snp is also called s2p files. one of smith chart is it works with only one freq and all other factors will based on it .now you have to use the q factor circle with the center freq ans then dfine the in and out impedance on smith chart and the add the lumped elements to match over the Wideband .

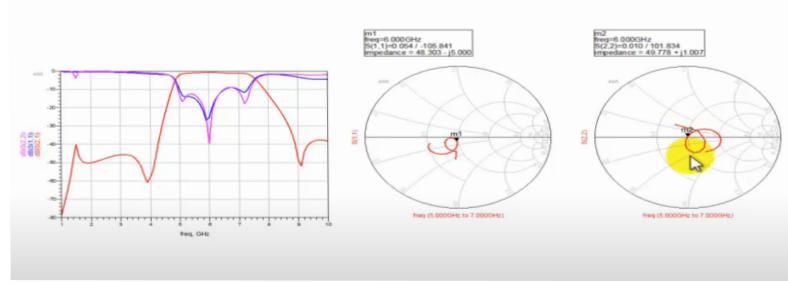


Figure 19: smith after widebend match the matching is not as good as expected as we didn't consider the freq dependeices on the BW

the frequency dependeices can be solved after matching with tthe optimization tool as on AWR by define optimization goals. on the optimization for the inductance it has L and R , do you should chose just L and C on the optimization tool no optimization for the R, so the wide band match is done for the Center freq but with the Q factor circuits, then apply optimization to get the best result.

Match Cascade this is very diffcult to measure the in and out of the two stages seperately as the are connected and we can only measure the S11 for the 1st stage and S22 for the 2nd stage, and to match we need S11 for the 2nd stage also S22 for the first stage and no port connected for this measure.

threre is a tool called SP probe with 50 ohm match at the two sides the pic define the proces fig. 20 it has left and write probe L.S11 is S22 for the 1st stage and R.S11 is the S11 for the single stage. for the sp probe you need to define you freq range. also check what other measurment can done with Sp probe as on the fig fig. 20 this means you have defined a port inside the design also you can use the impedance match tool on ADS it show the types of matching method by filters with LPF, HPF and Band pass filter.also with thr transmission lines and connect the network as on the figure

and aslo the match network topologies might be Diffrent. the topologies can be optimized and generated by impedance match utility tool on ADS on lec 7 with Anurag.

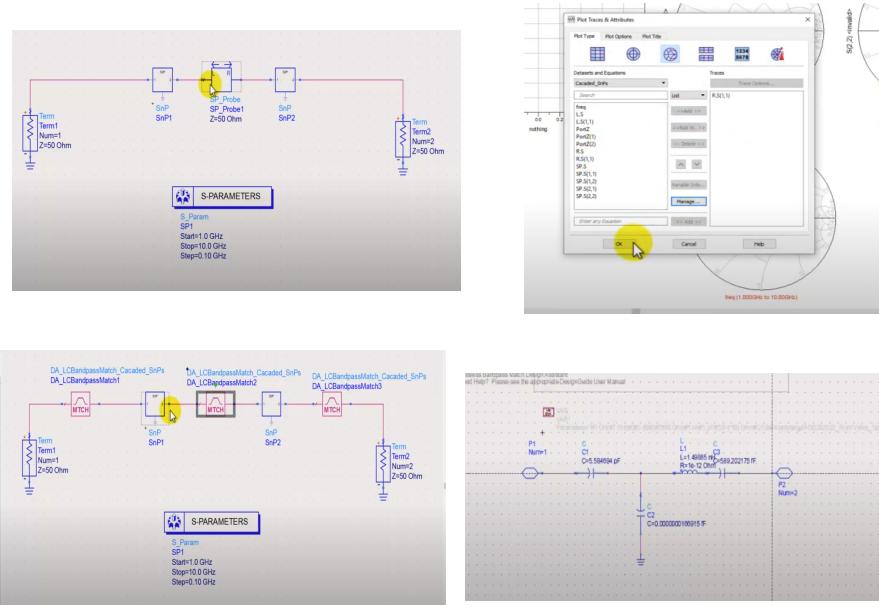


Figure 20: smith after widebend match the matching is not as good as expected as we didn't consider the freq dependeices on the BW

also after Cascade matching you need opotimization due to the freq dependeices the component that stops during optimization is because it reach the limit of the measur

Component tolerance **All the components on the design have a tolerance of +or - % more or less** this will need monto carlo and yiels analysis there is a video on the Anurag achannel about that after monto carlo simulation you will see the S11 for example it might be S22 or other you woll see many values on one curve which represent % change between the other curve this percent set up during simulation for the design.as fig. 19 then after you get this large number of the measurements make the yield analysis or yield optmization to get the central measument.

Anurag RF design 9

- some notes about the noise
- LNA Theory Fundamentals - Quick Review

What is a Low Noise Amplifier?

A low-noise amplifier (LNA) is an electronic amplifier that amplifies a very low-power signal without significantly degrading its signal-to-noise ratio. An amplifier will increase the power of both the signal and the noise present at its input, but the amplifier will also introduce some additional noise. LNAs are designed to minimize that additional noise. Designers can minimize additional noise by choosing low-noise components, operating points, and circuit topologies. Minimizing additional noise must balance with other design goals such as power gain, impedance matching. An LNA is a key component at the front-end of a radio receiver circuit to help reduce unwanted noise in particular. In most receivers, the overall NF is dominated by the first few stages of the RF front end.

By using an LNA close to the signal source, the effect of noise from subsequent stages of the receive chain in the circuit is reduced by the signal gain created by the LNA, while the noise created by the LNA itself is injected directly into the received signal.

The LNA boosts the desired signals' power while adding as little noise and distortion as possible. The work done by the LNA enables optimum retrieval of the desired signal in the later stages of the system.

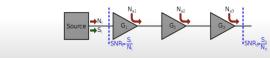
LNA Theory & Fundamentals – Quick Review

Friis formula is used to calculate the total noise factor of a cascade of stages, each with its own noise factor and power gain (assuming that the impedances are matched at each stage). The total noise factor can then be used to calculate the total noise figure.

The total noise factor is given as:

$$F_{\text{total}} = \frac{R_1}{G_1} + \frac{R_2}{G_2 G_1} + \frac{R_3}{G_3 G_2 G_1} + \dots + \frac{R_n}{G_n G_{n-1} \dots G_1}$$

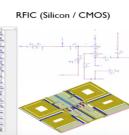
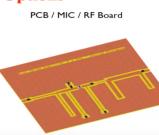
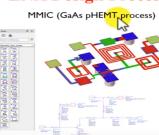
where R_i and G_i are the noise factor and available power gain, respectively, of the i -th stage, and n is the number of stages. Both magnitudes are expressed in dB, not in deciles.



$$\text{Noise Figure} = 10 \log_{10}(F) = 10 \log_{10} \left(\frac{\text{SNR}_i}{\text{SNR}_o} \right) = \text{SNR}_{i,\text{dB}} - \text{SNR}_{o,\text{dB}}$$

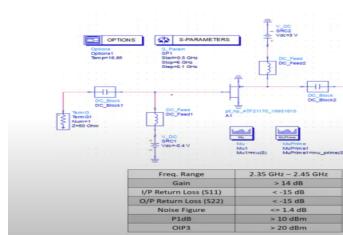
https://en.wikipedia.org/wiki/Friis_formulas_for_noise

LNA Design Process - Options



Transistor Models for LNA Designs

With Non-Linear Model



S2P File with Noise Data

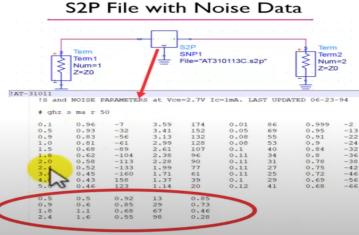


Figure 21: Stability for transistor and amplifier

- if you are lucky you will find the Nonlinear model of your transistor and if not you will have the S2p file that has noise parameter at the end of the file and mention the bias point and you will not be able to simulate the Nonlinear points p1dB and oip3
- with the nonlinear model first thinf add biasing for the transistor and get IV curves and check the point you look for it which should give as low as possible power consumption which is defined by $V_{ds} * I_d$ if with s parametr you can't so that as you have s parameter which is extracted at a particular bias point . with s parameter start from the stability point step 2

With the dielectric function ϵ , which describes the response of the material to external electromagnetic fields. $\epsilon = \epsilon_1 + i\epsilon_2$ is a complex function, which will in general depend strongly on the frequency of \vec{E} and also on the direction, if the material is anisotropic. The sometimes more intuitive complex refractive index \tilde{n} can be gained from ϵ through [?]:

$$\sqrt{\epsilon} = \tilde{n} = n + i\kappa \quad (1)$$

6.1 Key Paper 1

Discuss the first key paper. [1]

6.2 Key Paper 2

Discuss the second key paper. [2]

7 Conclusion

Summarize the key points discussed in the tutorial and their implications.

References

- [1] A. Author. Title of the key paper 1. *Journal Name*, 10(2):123–456, 2021.
- [2] B. Author. Title of the key paper 2. *Journal Name*, 11(3):789–1011, 2022.