

# Periodic Leaky-Wave Antenna for Millimeter Wave Applications Based on Substrate Integrated Waveguide

Feng Xu, *Senior Member, IEEE*, Ke Wu, *Fellow, IEEE*, and Xiupu Zhang, *Senior Member, IEEE*

**Abstract**—Substrate integrated waveguides (SIW) are built up of periodically arranged metallic via-holes or via-slots. The leakage loss of SIW structures increases with the distance between the via-holes or via-slots. An open periodic waveguide with a large via distance supports the propagation of leaky-wave modes and can thus be used for the design of a leaky-wave antenna. In this paper, this leakage loss is studied in detail and used to design a periodic leaky-wave antenna. The proposed concept represents an excellent choice for applications in the millimeter-wave band. Due to its versatility, the finite difference frequency domain method for periodic guided-wave or leaky-wave structures is used to analyze the characteristics of the proposed periodic leaky-wave antenna. Two modes ( $TE_{10}$  and  $TE_{20}$ ) are investigated and their different leaky-wave properties are analyzed. Based on the proposed leaky-mode analysis method, a novel periodic leaky-wave antenna at 28–34 GHz is designed and fabricated.

**Index Terms**—Finite difference frequency domain, periodic leaky-wave antenna, substrate integrated waveguide.

## I. INTRODUCTION

SUBSTRATE integrated waveguide (SIW) technology has been studied very extensively in recent years and has by now become a widely applied technique in planar microwave circuit design [1]–[4]. These waveguide-like structures are fabricated in planar form and are built up by periodically arranged metallic via-holes or via-slots [4] and take advantage of the well-known characteristics of conventional rectangular waveguides, namely, its high Q-factor and high power capacity, as well as its low losses. Though they have been studied for the use in antenna applications [5], [6], SIW structures have only been considered in the form of standard rectangular waveguides or cavities for slot antennas. In this paper, a novel concept is proposed that takes advantage of the increasing leakage loss for large via distances, which favors the forming of leaky-wave

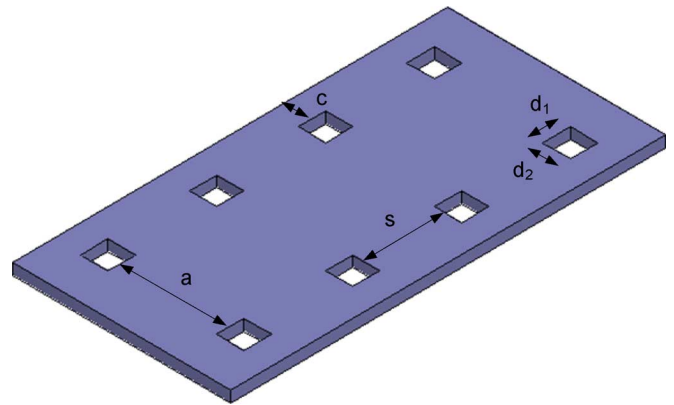


Fig. 1. Periodic leaky-wave antenna of SIW version.

modes in the structure. As a result, a periodic leaky-wave antenna can be designed based on SIW technology.

The operation principle of leaky-wave antennas has been well known for many years [7], [8]. There are two different kinds of leaky-wave antennas; one type is related to uniform guided-wave structures [9]–[11], while the second consists of an array of periodic guided-wave structures [12]–[15]. The first kind of leaky-wave antennas provides radiation into the forward quadrant and can yield scanning from broadside to forward end fire directions. The scanning range for periodic leaky-wave antennas reaches from backward end fire through broadside directions into a part of the forward quadrant. The dominant mode on the former type represents a fast wave, while the latter type is a slow wave structure. As a result, the dominant mode on periodic leaky-wave antennas does not radiate and radiation is achieved by using one of its space harmonics. A general SIW-based leaky-wave antenna architecture is shown in Fig. 1. Obviously, it belongs to the group of periodic leaky-wave antennas.

The analysis and design of leaky-wave antennas mainly consists of the extraction of two parameters, namely the phase constant  $\beta$  and the leakage constant  $\alpha$ . A number of numerical methods such as the transverse resonance method and the spectral-domain method have been used to extract the complex propagation constant. In this paper, the finite difference frequency domain (FDFD) method is selected due to its high versatility for analyzing the characteristics of the SIW leaky-wave antenna [16]–[18]. In recent years, this method has been successfully applied to extract the propagation characteristics of various types of SIW structures and is therefore directly applicable to the analysis of SIW leaky-wave antennas. For the analysis of this spe-

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F. Xu and K. Wu are with the Poly-Grames Research Center, Département de Génie Électrique, École Polytechnique de Montréal, Montréal, QC H3C 3A7, Canada (e-mail: feng.xu@polymtl.ca; ke.wu@polymtl.ca).

X. Zhang is with the Department of Electrical and Computer Engineering, Concordia University, Montréal, QC H3G 1M8, Canada (e-mail: xzhang@ece.concordia.ca).

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cific type of structure, the domain decomposition technique has to be used because the simulation of SIW leaky-wave antenna is carried out both in the substrate region and the air region. The two modes  $TE_{10}$  and  $TE_{20}$  in the SIW will be investigated in order to get their leakage mode characteristics and to obtain the appropriate space harmonics.

## II. FDFD ALGORITHM

When the FDFD method is used to resolve the characteristics of guided-wave structures, a nonsymmetrical standard eigenvalue problem is obtained if the equivalent resonant cavity model is used [17]. As an alternative, it is possible to use a standard FDFD method [16] by eliminating the longitudinal field components. In order to obtain more accurate results, in our case, a nonsymmetrical generalized eigenvalue problem is obtained [18],

$$\mathbf{A}\mathbf{x} = \gamma\mathbf{B}\mathbf{x} \quad (1)$$

where  $\gamma$  is the propagation constant, which may be a complex number depending on the type of problem. The vector  $\mathbf{x}$  is equal to  $\mathbf{x} = [\mathbf{h}_x, \mathbf{h}_y, \mathbf{e}_x, \mathbf{e}_y]^T$  for a wave propagation along the  $z$ -direction.

We introduce a shift-and-invert (SI) Arnoldi technique [19]–[21] in order to obtain a direct solution of the generalized eigenvalue problem in (1). The SI Arnoldi method can be used to compute a small number of eigenvalues close to a given shift and/or the associated eigenvectors of a large matrix pair. In the application of periodic guided-wave structures, we are interested in computing only some eigenvalues in the complex plane, which represent the complex propagation constants. In (1), for eigenvalues close to a shift  $\sigma$ , we obtain

$$\mathbf{A}\mathbf{x} = \gamma\mathbf{B}\mathbf{x} \Leftrightarrow (\mathbf{A} - \sigma\mathbf{B})\mathbf{x} = (\gamma - \sigma)\mathbf{B}\mathbf{x}. \quad (2)$$

Thus

$$(\mathbf{A} - \sigma\mathbf{B})^{-1}\mathbf{B}\mathbf{x} = \theta\mathbf{x} \quad (3)$$

where

$$\theta = \frac{1}{\gamma - \sigma}.$$

As shown in Fig. 2, the entire simulation domain includes the substrate sub-domain and the air sub-domain in the case of leaky-wave antennas. As a result, the concept of domain decomposition is introduced in the simulation.

## III. PARAMETRIC ANALYSIS

It is well known that the wave propagation for the dominant mode in periodic leaky-wave antennas is slow ( $\beta > k_0$ ) relative to free-space velocity, and the dominant mode itself does not

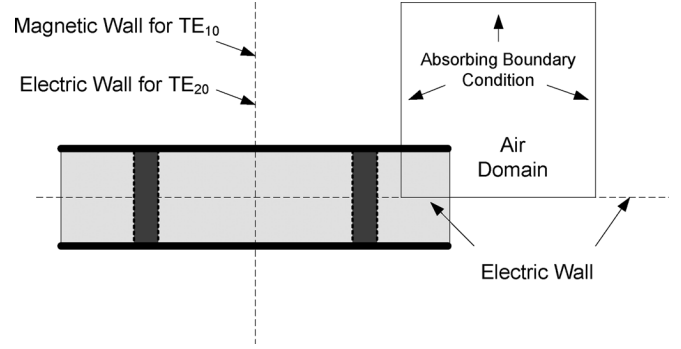


Fig. 2. Transversal view of the SIW simulation domain.

radiate. The radiation of periodic leaky-wave antennas is originating from space harmonics introduced by periodicity,

$$\beta_n d = \beta_0 d + 2n\pi \quad (4)$$

where  $d$  is the period, and  $\beta_0$ , the fundamental space harmonic, represents the propagation constant  $\beta$  of the dominant mode for a periodic guided-wave structure. When  $\beta_n$  takes different values, the related space harmonic can be forward or backward in nature. The necessary condition for the radiation of a space harmonic is

$$\frac{\beta_n}{k_0} < 1. \quad (5)$$

In a practical antenna design, usually only a single main radiated beam is needed and thus  $\beta_{-1}$  is selected. As a result, when the frequency increases, the  $\beta_{-1}$  space harmonic starts to radiate from a backward end fire direction. With a further increase in frequency, the beam moves from the backward end fire direction into the back quadrant. For even higher frequencies, the beam moves toward broadside radiation, then traverses broadside direction, and moves into the forward quadrant. However, the range in the forward quadrant is usually limited by the emergence of the  $\beta_{-2}$  beam at the backward end fire direction or by a higher guided-wave mode [8].

The beam direction of periodic leaky-wave antennas can be calculated from

$$\sin \theta_m \approx \frac{\beta_{-1}}{k_0} \quad (6)$$

where  $\theta_m$  is the maximum beam angle measured in broadside direction and

$$\beta_{-1} = \beta_0 - \frac{2\pi}{d}. \quad (7)$$

The next section includes a detailed discussion of the radiation characteristics for the two leakage modes  $TE_{10}$  and  $TE_{20}$  in SIW structures.

### A. Leaky-Wave Mode Related to the TE<sub>10</sub> Mode

For the analysis of this specific case, a magnetic wall is introduced in the center of the SIW as shown in Fig. 2. The propagation constant of the dominant mode can be approximated as

$$\beta_0 = \frac{2\pi}{\lambda} \sqrt{1 - \left(\frac{\lambda}{2a'}\right)^2} \quad (8)$$

where  $a'$  is the equivalent width of the waveguide and is larger than the inner width  $a$  (as shown in Fig. 1) of an SIW [4], [22]. From (5) and (8) we obtain the condition, for which the dominant mode does not radiate as

$$\frac{\beta_0}{k_0} = \sqrt{\epsilon_r} \sqrt{1 - \left(\frac{\lambda}{2a'}\right)^2} > 1. \quad (9)$$

Obviously, if the condition is fulfilled at a certain low frequency, the dominate mode does not radiate at higher frequencies. The permittivity of the substrate is selected according to the low frequency of leaky-wave antennas to  $\epsilon_r > 2$ .

The phase constant for the TE<sub>10</sub> leaky-wave mode is obtained from (7) and (8) as

$$\beta_{-1} = \frac{2\pi}{\lambda} \sqrt{1 - \left(\frac{\lambda}{2a'}\right)^2} - \frac{2\pi}{d}. \quad (10)$$

From (10), we can conclude that the period  $d$  is a key factor in the design of leaky-wave antennas as it directly defines the antenna's frequency range with a smaller period  $d$  resulting in a higher operating frequency. Although the design of periodic leaky-wave antennas also depends on the leakage constant, we can use (9) and (10) to determine its frequency range and select an approximate value for the substrate permittivity.

In a next step, the FDFD method will be used to extract the leakage constant and the phase constant of SIW leaky-wave antennas accurately. As shown in Fig. 1, the dimensions are selected to an SIW width  $a = 10$  mm, rectangular metal slot dimensions  $d_1 = 0.8$  mm and  $d_2 = 0.8$  mm, and a distance between the slots  $s = 4.8$  mm. This yields a period length  $d = s + d_1 = 5.6$  mm. An RT/duroid 5880 substrate with a thickness  $t$  of 0.787 mm, a permittivity  $\epsilon_r = 2.2$ , and a loss tangent  $\tan \delta = 0.009$  is selected in the simulation.

The value of the phase constant is very important in determining the main beam direction, as well as for identifying single or multi beam operation. For the presented analysis we assume an infinitely extended substrate ( $c$  is infinite) in order to highly simplify the simulation model. The phase constants obtained from these approximate equations are very similar to the results obtained for the case of a finite substrate. However, the main beam direction needs to be multiplied with a factor  $(\epsilon_0/\epsilon)^{0.5}$  according to the Snell's law. Please note that if  $c$  is infinite, the dominant mode is a fast wave. In this analysis, we only focus on the calculation of the first space harmonics.

Figs. 3 and 4 show the angle of maximum radiation calculated from (6) and the normalized leakage constant. In Fig. 3, a

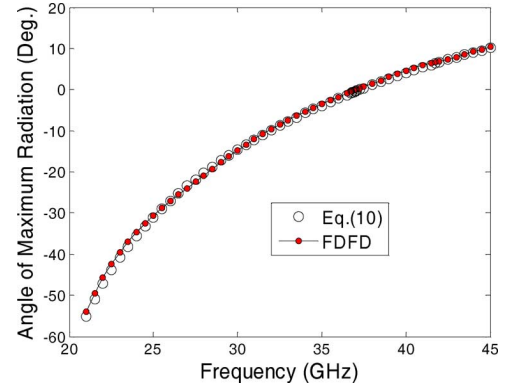


Fig. 3. Comparison of the angles of maximum radiation for the SIW leaky-wave antenna for the TE<sub>10</sub> mode,  $s = 4.8$  mm and  $d_1 = 0.8$  mm.

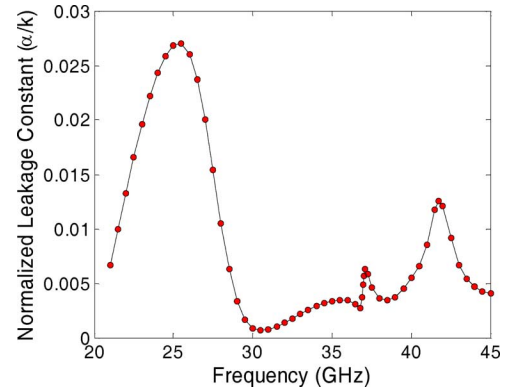


Fig. 4. Normalized leakage constant for the SIW leaky-wave antenna for the TE<sub>10</sub> mode,  $s = 4.8$  mm and  $d_1 = 0.8$  mm.

comparison of the results of the FDFD method and the approximate relation in (10) ( $a' = 11$  mm) illustrates that the latter is a suitable approximation for evaluating the phase constant of SIW leaky-wave antennas. From Fig. 4, we observe a stop band that emerges for beam angles close to zero.

For modified dimensions  $s = 4.0$  mm and  $d_1 = 1.6$  mm (note that the overall periodical distance  $d = s + d_1 = 5.6$  mm keeps unchanged), the angle of maximum radiation and the normalized leakage constant calculated with the FDFD method are shown in Figs. 5 and 6, respectively. As the period  $d$  keeps unchanged, the phase constants are expected to remain almost constant, which is proved by comparison of the results in Figs. 3 and 5. On the contrary, the leakage constants in Figs. 4 and 6 are different. However, the influence of the stop band is very small in both cases.

### B. Leaky-Mode Related to the TE<sub>20</sub> Mode

For the analysis of the TE<sub>20</sub> mode, an electric wall is introduced in the center of the SIW as shown in Fig. 2. The propagation constant of the dominant mode can be calculated approximately as

$$\beta_0 = \frac{2\pi}{\lambda} \sqrt{1 - \left(\frac{\lambda}{a'}\right)^2}. \quad (11)$$

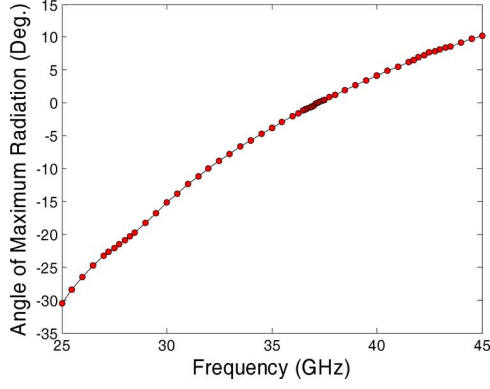


Fig. 5. Angles of maximum radiation of the SIW leaky-wave antenna for TE<sub>10</sub> mode,  $s = 4.0$  mm and  $d_1 = 1.6$  mm.

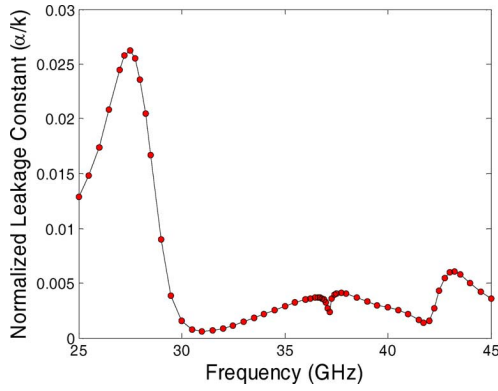


Fig. 6. Normalized leakage constant of the SIW leaky-wave antenna for TE<sub>10</sub> mode,  $s = 4.0$  mm and  $d_1 = 1.6$  mm.

From (5) and (11), we obtain the condition, for which the dominant mode does not radiate as

$$\frac{\beta_0}{k_0} = \sqrt{\epsilon_r} \sqrt{1 - \left(\frac{\lambda}{a'}\right)^2} > 1. \quad (12)$$

By comparing (9) and (12), we observe that the lowest frequency of the TE<sub>20</sub> mode, for which the dominant mode does not radiate, is higher than that of the TE<sub>10</sub> mode. Therefore, it is better to use a substrate with higher permittivity.

The phase constant of the leaky-wave mode can be calculated from (7) and (11) as

$$\beta_{-1} = \frac{2\pi}{\lambda} \sqrt{1 - \left(\frac{\lambda}{a'}\right)^2} - \frac{2\pi}{d}. \quad (13)$$

According to (13), the frequency for obtaining a certain beam angle in TE<sub>20</sub> mode is higher than in TE<sub>10</sub> mode.

The FDFD method can also be used in the case of TE<sub>20</sub> mode for extracting the leakage constant and phase constant of SIW leaky-wave antennas. The dimensions are selected to an SIW width  $a = 10$  mm, rectangular metal slot dimensions  $d_1 = 0.8$  mm and  $d_2 = 0.8$  mm, and a slot distance  $s = 4.8$  mm, which yields a period  $d = s + d_1 = 5.6$  mm. Again we assume an infinitely extended substrate ( $c = \infty$ ) for the simulation.

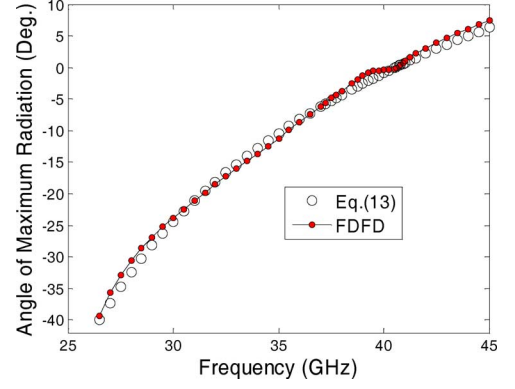


Fig. 7. Comparison of the angles of maximum radiation of the SIW leaky-wave antenna for the TE<sub>20</sub> mode,  $s = 4.8$  mm and  $d_1 = 0.8$  mm.

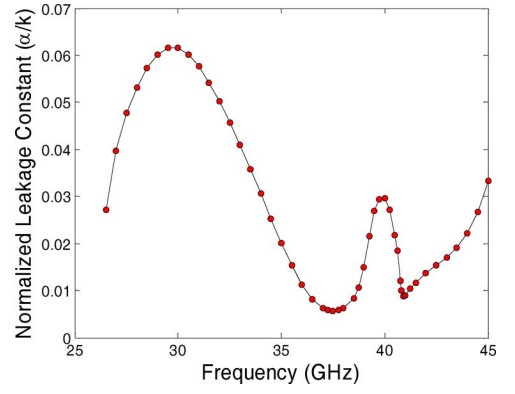


Fig. 8. Normalized leakage constant of the SIW leaky-wave antenna for the TE<sub>20</sub> mode,  $s = 4.8$  mm and  $d_1 = 0.8$  mm.

An RT/duroid 5880 substrate with a thickness  $t$  of 0.787 mm is selected.

Figs. 7 and 8 show the angle of maximum radiation and the normalized leakage constant, respectively. In Fig. 7, a comparison of the FDFD method and (13) ( $a' = 11$  mm) illustrate once more that the approximation in (12) is suitable to evaluate the phase constant of SIW leaky-wave antennas. Furthermore, from Fig. 8, we also observe that the influence of the stop band is small.

For different dimensions  $s = 4.0$  mm and  $d_1 = 1.6$  mm ( $d = s + d_1 = 5.6$  mm keeps unchanged), the angle of maximum radiation and the normalized leakage constant obtained from the FDFD method are shown in Figs. 9 and 10, respectively. Again, for an unchanged period  $d$ , the phase constants remain almost constant, which is proved by comparison between the results in Figs. 7 and 9. The leakage constants shown in Figs. 8 and 10 are again different. A comparison of Figs. 4 and 8, as well as Figs. 6 and 10, leads to the conclusion, that the radiation characteristics of the TE<sub>20</sub> mode are better than for the TE<sub>10</sub> mode.

### C. Finite Substrate

In practical applications  $c$  is finite, as shown in Fig. 1. This section describes an analysis of the impact of different values for  $c$  on the characteristics of SIW leaky-wave antennas.

Based on the analysis results in the previous section, a leaky-wave antenna operating in TE<sub>20</sub> mode will be investigated. The dimensions are the same as for the case in Fig. 7, i.e., an SIW

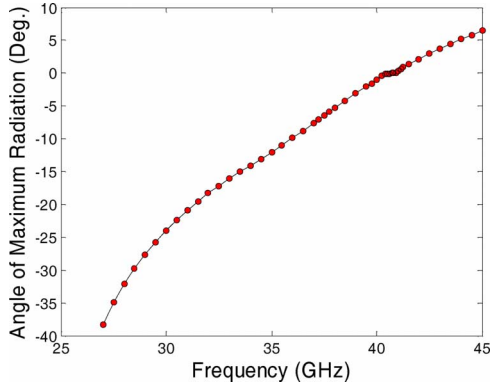


Fig. 9. Angles of maximum radiation of the SIW leaky-wave antenna for the  $TE_{20}$  mode,  $s = 4.0$  mm and  $d_1 = 1.6$  mm.

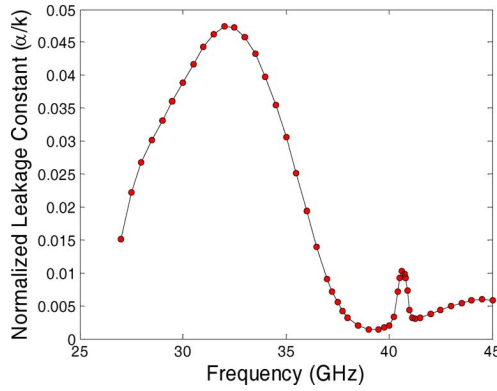


Fig. 10. Normalized leakage constant of the SIW leaky-wave antenna for the  $TE_{20}$  mode,  $s = 4.0$  mm and  $d_1 = 1.6$  mm.

width  $a = 10$  mm, rectangular metal slot dimensions  $d_1 = 0.8$  mm and  $d_2 = 0.8$  mm, a slot distance  $s = 4.8$  mm, a permittivity  $\epsilon_r = 2.2$ , a loss tangent  $\tan \delta = 0.009$ , and a substrate thickness  $t = 0.787$  mm. Three different values for  $c$  are investigated, i.e.,  $c = 2.1$  mm,  $2.2$  mm, and  $2.3$  mm. As shown in Fig. 2, the entire FDFD simulation domain includes the substrate sub-domain and the air sub-domain and the concept of domain decomposition is introduced into the simulation. Fig. 11 shows the normalized leakage constants for the three selected  $c$  values obtained from the FDFD method. From Fig. 11, we observe that the antenna has the best leakage behavior for  $c = 2.2$  mm.

The angle of maximum radiation for  $c = 2.2$  mm is shown in Fig. 12. Again, (13) is used for an approximate evaluation of the angle. Note, that for this case the wave number for free space radiation in (6) needs to be used. In addition, according to Snell's law, the angle of maximum radiation needs to be multiplied with a factor  $(\epsilon_0/\epsilon)^{0.5}$  at the interface between the substrate and free space. From Fig. 12, it is observed that multiple reflections and refractions occurring at the interface have only a small influence on the phase constant. However, their impact on the leakage constant is relative large.

#### IV. MEASUREMENT

Based on the analysis in Section III, a  $TE_{20}$  mode leaky-wave antenna is designed and fabricated. Although the leakage char-

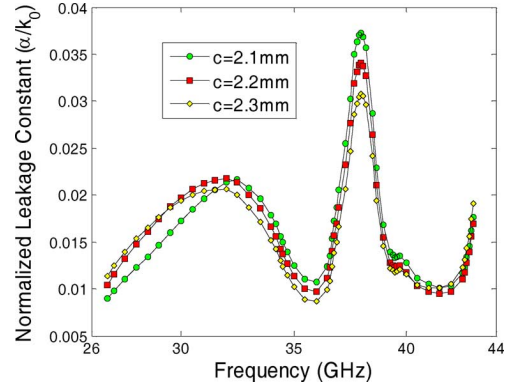


Fig. 11. Normalized leakage constant of the SIW leaky-wave antenna for the  $TE_{20}$  mode,  $s = 4.8$  mm,  $d_1 = 0.8$  mm.

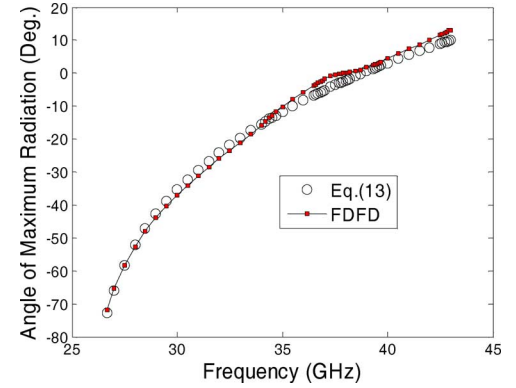


Fig. 12. Angles of maximum radiation of the SIW leaky-wave antenna in free space radiation for the  $TE_{10}$  mode,  $s = 4.8$  mm,  $d_1 = 0.8$  mm and  $c = 2.2$  mm.

acteristics in Fig. 11 are not as good as for the result presented in Fig. 8, an SIW leaky-wave antenna operating in the range of 28–34 GHz is designed in order to verify the conception and the design rules for SIW leaky-wave antenna proposed here. The dimensions are selected according to the values given in Fig. 11, and  $c$  is selected to  $2.2$  mm.

##### A. Feed

The excitation of the  $TE_{20}$  mode is realized by combining two  $TE_{10}$  modes with opposite phases. As shown in Fig. 13, a microstrip line equally divides the input signal in two parts and excites the  $TE_{10}$  mode in two narrow SIW branches. The travelling wave is a quasi-TEM mode on the microstrip line and a  $TE_{10}$  mode in the SIW. In order to realize the opposite phase combination of the two  $TE_{10}$  modes, different lengths of microstrip and SIW are selected according to

$$\frac{2\pi}{\lambda_0} \sqrt{\epsilon_e} \cdot \Delta l - \frac{2\pi}{\lambda} \sqrt{1 - \left(\frac{\lambda}{2a_0}\right)^2} \cdot \Delta l \approx \pi \quad (14)$$

where  $\Delta l = l_1 - l_0$  as indicated in Fig. 13, and  $\epsilon_e$  is the effective permittivity of the microstrip. Finally, the two SIW branches are combined into a wide SIW branch representing the leaky-wave antenna in order to excite its required  $TE_{20}$  mode.



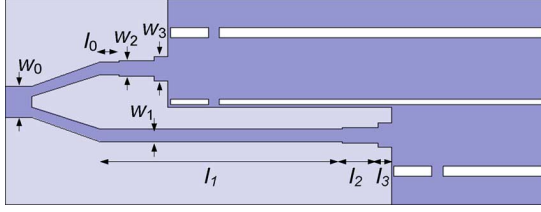
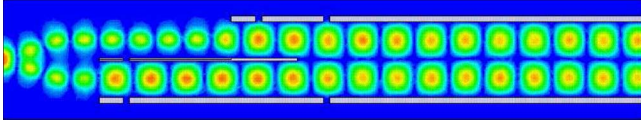
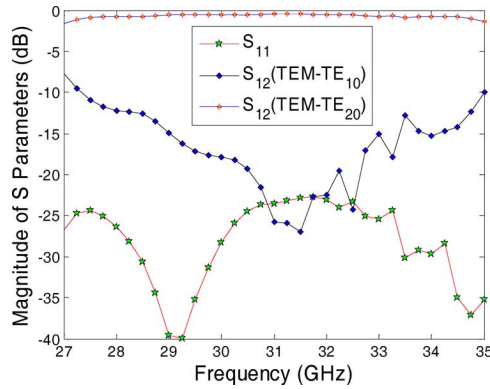
Fig. 13. Topology of TE<sub>20</sub> mode feed.

Fig. 14. Field distribution of feed extracted from Ansoft HFSS.

Fig. 15. *S* parameters of feed calculated with HFSS.

The dimensions of the feed are selected to  $w_0 = 2.4$  mm,  $w_1 = 1$  mm,  $w_2 = 1.2$  mm,  $w_3 = 1.9$  mm,  $l_0 = 1.4$  mm,  $l_1 = 17.9$  mm,  $l_2 = 2.6$  mm, and  $l_3 = 1$  mm. The width  $a_0$  of the two narrow SIW branches is 4.8 mm.

The simulation of the proposed structure is carried out with the help of Ansoft HFSS, offering a significant reduction in simulation time. Fig. 14 shows the calculated field distribution and confirms the development of the desired TE<sub>20</sub> mode in the wide SIW branch at a central frequency of 31 GHz. In addition, a detailed *S*-parameter simulation for the feed design in Figs. 13 and 14 is performed. Two ports, one for a quasi-TEM mode at the input of the microstrip line, and one for TE<sub>10</sub> and TE<sub>20</sub> modes at the end of the wide SIW branch are introduced. Fig. 15 shows the *S*-parameter results obtained from HFSS, which prove a good performance in terms of input matching of the feed as well as suppression of the TE<sub>10</sub> mode.

### B. Measurement of the SIW Leaky-Wave Antenna

The dimensions of the presented leaky-wave antenna have been outlined in Section IV. A Rogers RT/Duroid 5880 with  $\epsilon_r = 2.2$  and  $\tan \delta = 0.009$  is used for fabrication. According to the simulated leakage constant calculated from the FDFD method, the antenna length is selected to  $L/\lambda_0 \approx 7$ . The manufactured prototype of the SIW periodic leaky-wave antenna is shown in Fig. 16 and the simulated and measured results for the return

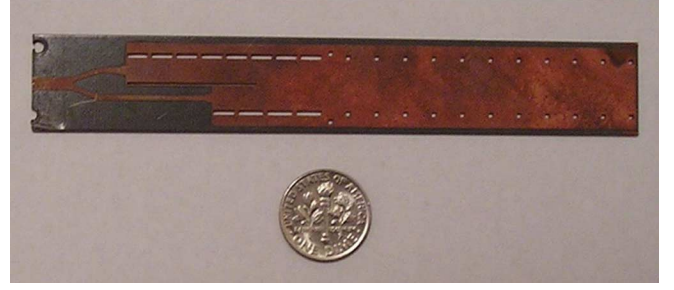
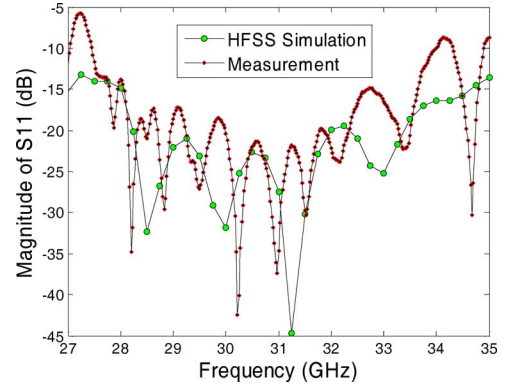
Fig. 16. Photograph of the manufactured the SIW TE<sub>20</sub> leaky-wave antenna.

Fig. 17. Measured and simulated return loss of the leaky-wave antenna.

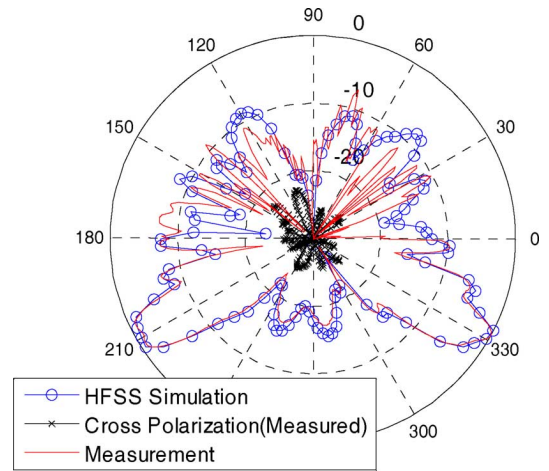


Fig. 18. Measured and simulated H plane pattern at 31 GHz.

loss are shown in Fig. 17. The return loss is lower than  $-15$  dB over the entire frequency range of 28–34 GHz.

The simulated and measured far-field patterns at the center frequency of 31 GHz in the H-plane (the plane of the substrate) are shown in Fig. 18. As expected from the results obtained in Fig. 12, the antenna radiates at an angle of about  $-30^\circ$ . Furthermore, the measured maximum cross polarization in the plane is reasonably low (less than  $-20$  dB). The gain in simulation and measurement are 9.514 dB and 9.3 dB at 31 GHz, respectively. The E-plane (the plane vertical to the propagation direction) pattern is shown in Fig. 19. A good agreement for the radiation patterns in Figs. 18 and 19 verifies the design procedure and analysis of the presented SIW leaky-wave antenna.

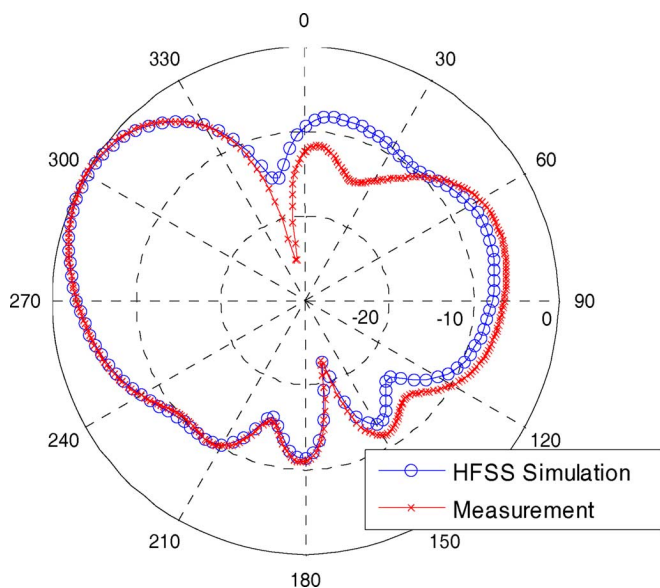


Fig. 19. Measured and simulated E plane pattern at 31 GHz.

## V. CONCLUSION

The simulation and measurement results have validated the proposed design and analysis method of an SIW-based periodic leaky-wave antenna. The design of such an antenna is based on the leakage loss of SIW structures, which increases with distance between the via-holes or via-slots. An open periodic waveguide with a large via distance supports the propagation of leaky-wave modes and can therefore be used for the design of a leaky-wave antenna. The developed SIW-based structure is very suitable for applications in the millimeter-wave band. Important design characteristics have been identified, such as the better radiation properties of the  $TE_{20}$  mode over the  $TE_{10}$  mode. Moreover, the substrate permittivity and the periodical distance are key parameters for the performances such as the directivity, operating frequency and efficiency. Future work includes a more detailed investigation for solving the problem related to the observed stop band.

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**Feng Xu** (M'05–SM'09) was born in Jiangsu, China. He received the B.S. degree in radio engineering from Southeast University, Nanjing, China, in 1985, the M.S. degree in microwave and millimeter-wave theory and technology from the Nanjing Research Institute of Electronics and Technology, Nanjing, in 1998, and the Ph.D. degree in radio engineering from Southeast University, Nanjing, in 2002.

From 1985 to 1996, he was with the Nanjing Research Institute of Electronics and Technology, where he conducted research in the areas of antenna and RF circuits design. Since 2002, he has been with the Poly-Grames Research Center, École Polytechnique, Montréal, QC, Canada, where he has been a Postdoctoral Researcher and is currently a Research Associate. His current research interests include numerical methods for electromagnetic field problem and advanced microwave and millimeter-wave circuits and components.



**Ke Wu** (M'87–SM'92–F'01) received the B.Sc. degree (with distinction) in radio engineering from Nanjing Institute of Technology (now Southeast University), Nanjing, China, in 1982 and the D.E.A. and Ph.D. degrees in optics, optoelectronics, and microwave engineering (with distinction) from Institut National Polytechnique de Grenoble (INPG) and University of Grenoble, France, in 1984 and 1987, respectively.

He is currently a Professor of electrical engineering, and Tier-I Canada Research Chair in RF and Millimeterwave Engineering at Ecole Polytechnique (University of Montreal). He has (co)-authored over 680 referred papers, a number of books/book chapters and patents. His current research interests involve substrate integrated circuits (SICs), antenna arrays, advanced CAD and modeling techniques, and development of low-cost RF and millimeter-wave transceivers. He is also interested in the modeling and design of microwave photonic circuits and systems. He serves on the Editorial Board of *Microwave Journal*, *Microwave and Optical Technology Letters*, and Wiley's *Encyclopedia of RF and Microwave Engineering*. He is an Associate Editor of *International Journal of RF and Microwave Computer-Aided Engineering (RFMiCAE)*.

Dr. Wu also holds a number of Visiting (Guest) and Honorary Professorships at various universities including the first Cheung Kong Endowed Chair Professorship at Southeast University, the first Sir Yue-Kong Pao Chair Professorship at Ningbo University, and Honorary Professorship at Nanjing University of Science and Technology and City University of Hong Kong. He has been director of the Poly-Grames Research Center and has recently become the Founding Director of "Centre de recherche en électronique radiofréquence" (CREER) of Quebec. He is a member of Electromagnetics Academy, the Sigma Xi Honorary Society, and the URSI. He has held many positions in and has served on various international committees, including co-chair of the Technical Program Committee (TPC) for 1997 and 2008 Asia-Pacific Microwave Conferences (APMC), General Co-Chair of 1999 and 2000 SPIE's Inter. Symposia on Terahertz and Gigahertz Electronics and Photonics, General Chair of 8th Inter. Microwave and Optical Technology (ISMOT'2001), TPC Chair of 2003 IEEE Radio and Wireless Conference (RAWCON'2003), General Co-Chair of RAWCON'2004, Co-Chair of 2005 APMC Inter. Steering Committee, General Chair of 2007 URSI Inter. Symp. on Signals, Systems and Electronics (ISSSE), and General Co-Chair of 2008 and 2009 Global Symposia on Millimeter-Waves, and Inter. Steering Committee Chair of 2008 Inter. Conference on Microwave and Millimeter-Wave Technology. In particular, he will be General Chair of 2012 IEEE MTT-S International Microwave

Symposium (IMS). He has served on Editorial or Review Boards of various technical journals, including the IEEE TRANSACTIONS ON MICROWAVE THEORY AND TECHNIQUES, the IEEE TRANSACTIONS ON ANTENNAS AND PROPAGATION, and the IEEE MICROWAVE AND WIRELESS COMPONENTS LETTERS. He served on the Steering Committee for the 1997 joint IEEE AP-S/URSI Inter. Symp. and the TPC for the IEEE MTT-S Inter. Microwave Symp. He is currently chair of the joint IEEE chapters of MTT-S/APS/LEOS in Montreal. He is an elected MTT-S AdCom member for 2006–2012 and was Chair of the IEEE MTT-S Transnational Committee. He is Chair of the newly formed IEEE MTT-S Member and Geographic Activities (MGA) Committee. He was the recipient of a URSI Young Scientist Award, IEE Oliver Lodge Premium Award, Asia-Pacific Microwave Prize, IEEE CCECE Best Paper Award, University Research Award "Prix Poly 1873 pour l'Excellence en Recherche" presented by the Ecole Polytechnique on the occasion of its 125th anniversary, Urgel-Archambault Prize (the highest honor) in the field of physical sciences, mathematics and engineering from ACFAS, and 2004 Fessenden Medal of IEEE Canada. In 2002, he became the first recipient of the IEEE MTT-S Outstanding Young Engineer Award. He is Fellow of the Canadian Academy of Engineering (CAE) and Fellow of the Royal Society of Canada (The Canadian Academy of the Sciences and Humanities).



**Xiupu Zhang** (SM'07) received the B.Sc. degree from Harbin University of Science and Technology, Harbin, China, in 1983, the M.Sc. degree from Beijing University of Posts and Telecommunications, Beijing, China, in 1988, and the Ph.D. degree from the Technical University of Denmark, Lyngby Denmark, in 1996, all in electrical engineering.

Following his Ph.D. study, he worked as a Research Fellow at Chalmers University of Technology, Goteborg, Sweden, for one and a half of years. Prior to joining Concordia University in June 2002, he had

worked in fiber-optics industry in China, Canada, and the USA for about 10 years. Currently, he is a Professor in Department of Electrical and Computer Engineering, Concordia University, Quebec Canada. His current research interests include optical fiber transmission, radio-over-fiber systems, quantum dot semiconductors, THz generation and broadband optical sources.

Dr. Zhang is a member of OSA.