DSP & Digital Filters

Lecture 1 z-Transform

DR TANIA STATHAKI

READER (ASSOCIATE PROFESSOR) IN SIGNAL PROCESSING
IMPERIAL COLLEGE LONDON

Laplace transform: generalised frequency transformation.

Continuous-time signals

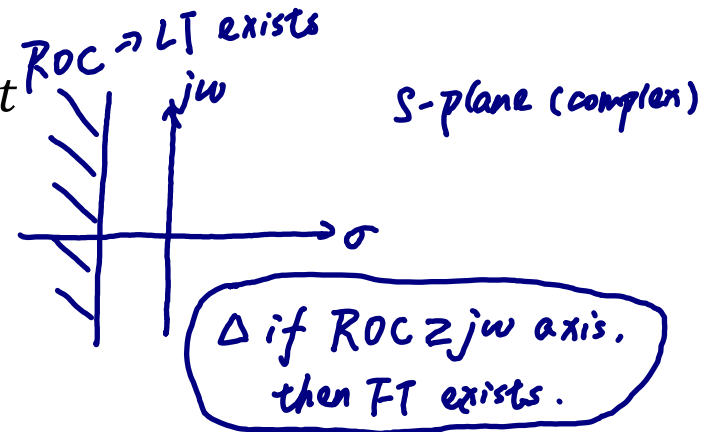*(all signals have LT but not all have FT).*

- Recall that in order to describe a continuous-time signal $x(t)$ in frequency domain we use:

☐ The Continuous-Time Fourier Transform (or Fourier Transform):

$$X(\omega) = \int_{-\infty}^{\infty} x(t)e^{-j\omega t}dt$$

ROC → LT exists

jw

S-plane (complex)

☐ The Laplace Transform

$$X(s) = \int_{-\infty}^{\infty} x(t)e^{-st}dt$$

S = σ + jw

σ

Δ if ROC ⊇ jw axis, then FT exists.

- The above transforms and their basic properties are considered known in this course.

- If you have doubts please consult any book on Signals and Systems.

Discrete-time signals
The z-transform derived from the Laplace transform

$$x[n] = x(nT)$$
$$x(t) = \sum_n x[n]\delta(t-nT)$$

samples
$x[n]$

- Consider a discrete-time signal $x(t)$ sampled every T seconds.

$$x(t) = x_0\delta(t) + x_1\delta(t-T) + x_2\delta(t-2T) + x_3\delta(t-3T) + \cdots$$

- Recall that in the Laplace domain we have:

LT: $X(s) = \int_{-\infty}^{+\infty} x[v] e^{-st} dt$

$$\mathcal{L}\{\delta(t)\} = 1$$
$$\mathcal{L}\{\delta(t-T)\} = e^{-sT}$$

$x(t) = \frac{1}{k}\sum_{i=0}^{k-1}\cos(\omega_i t)$

$= \begin{cases} 1, & t=0 \\ \to 0, & t\neq 0 \end{cases}$
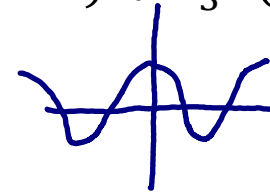
if $k \to \infty$, $x(t) \to \delta(t)$.

- Therefore, the Laplace transform of $x(t)$ is:

$$X(s) = x_0 + x_1 e^{-sT} + x_2 e^{-s2T} + x_3 e^{-s3T} + \cdots$$

- Now define $z = e^{sT} = e^{(\sigma+j\omega)T} = e^{\sigma T}\cos\omega T + j e^{\sigma T}\sin\omega T$.

- Finally, define

$$X[z] = x_0 + x_1 z^{-1} + x_2 z^{-2} + x_3 z^{-3} + \cdots$$

z^{-1}: the sampling period delay operator

$\delta(t-T) \leftrightarrow e^{-sT} = z^{-1}$: delay by a sampling period.

- From the Laplace time-shift property, we know that an additional term $z = e^{sT}$ in the Laplace domain, corresponds to time-advance by T seconds (T is the sampling period) of the original function in time.

- Accordingly, $z^{-1} = e^{-sT}$ corresponds to a time-delay of one sampling period.

- As a result, all sampled data (and discrete-time systems) can be expressed in terms of the variable z.

- More formally, the **unilateral $z-$transform** of a causal sampled sequence:

$$x[n] = \{x[0], x[1], x[2], x[3], \dots\}$$

is given by:

$$X[z] = x_0 + x_1 z^{-1} + x_2 z^{-2} + x_3 z^{-3} + \cdots = \sum_{n=0}^{\infty} x[n] z^{-n}, \; x_n = x[n]$$

- The **bilateral $z-$transform** for any sampled sequence is:

$$X[z] = \sum_{n=-\infty}^{\infty} x[n] z^{-n}$$

$$X[z] = \sum_{n=0}^{\infty} \gamma^n z^{-n} = \sum_{n=0}^{\infty} \left(\frac{r}{z}\right)^n = \frac{1}{1-\frac{r}{z}} = \frac{z}{z-r}, \left|\frac{r}{z}\right| < 1$$

ROC: $|z| > |r|$

Example: Find the $z-$transform of $x[n] = \gamma^n u[n]$

- Find the $z-$transform of the **causal** signal $\gamma^n u[n]$, where γ is a constant.
- By definition:

$$X[z] = \sum_{n=-\infty}^{\infty} \gamma^n u[n] z^{-n} = \sum_{n=0}^{\infty} \gamma^n z^{-n} = \sum_{n=0}^{\infty} \left(\frac{\gamma}{z}\right)^n$$

$$= 1 + \left(\frac{\gamma}{z}\right) + \left(\frac{\gamma}{z}\right)^2 + \left(\frac{\gamma}{z}\right)^3 + \cdots$$

- We apply the geometric progression formula:

$$1 + x + x^2 + x^3 + \cdots = \frac{1}{1-x}, |x| < 1$$

- Therefore,

$$X[z] = \frac{1}{1-\frac{\gamma}{z}}, \left|\frac{\gamma}{z}\right| < 1$$

$$= \frac{z}{z-\gamma}, |z| > |\gamma|$$

- We notice that the $z-$transform exists for certain values of z. These values form the so called Region-of-Convergence (ROC) of the transform.

Example: Find the $z-$transform of $x[n] = \gamma^n u[n]$ cont.

- Observe that a simple rational equation in z-domain corresponds to an infinite sequence of samples in time-domain.

- The figures below depict the signal in time (left) for $|\gamma| < 1$ and the ROC, shown with the shaded area, within the $z-$plane.

$x[n]$ absolutely summable : $|r| < 1$

ROC: $|z| > |r|$

∴ ROC ⊇ unit circle.
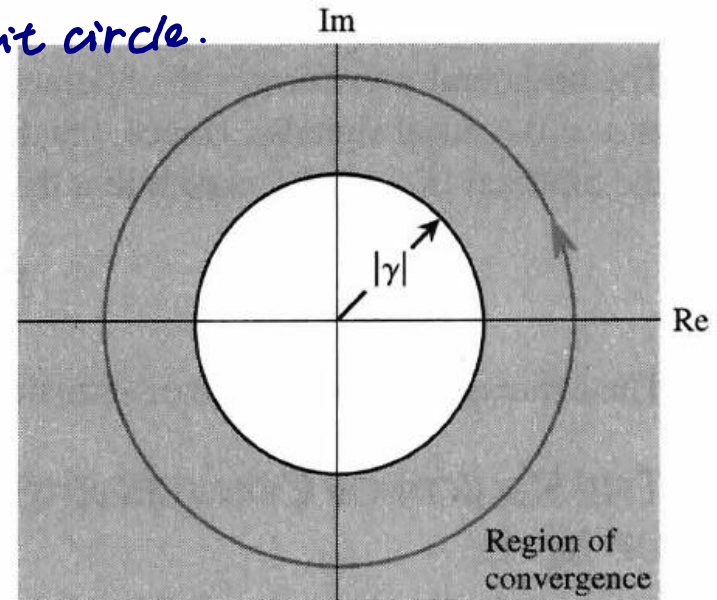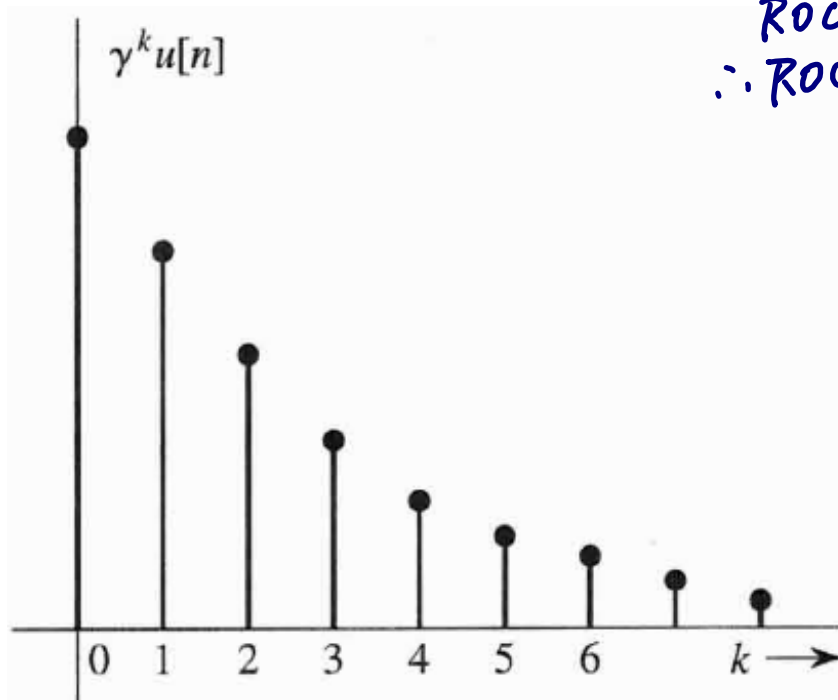
$$x[n] = \sum_{i=1}^{k} r_i^n u[n]$$

$$X(z) = \sum_{n=-\infty}^{+\infty} x[n] z^{-n} = \sum_{n\geq 0}^{+\infty} \sum_{i=1}^{k} r_i^n z^{-n} = \left(\sum_{i=1}^{k} \frac{z}{z-r_i} \right), \quad |z| > |r_i|_{max}$$

poles at $z = r_i$

Generic form of a causal signal

$r \neq i$

$r_i \sim i$

- Consider the causal signal $x[n] = \sum_{i=1}^{K} \gamma_i^n u[n]$ with $X(z) = \sum_{i=1}^{K} \frac{z}{z-\gamma_i}$.

- In that case the ROC is the intersection of the ROCs of the individual terms, i.e., the intersection of the sets $|z| > |\gamma_i|$ i.e., ROC: $|z| > |\gamma_{\max}|$

- In case that $x[n]$ is the impulse response of a system, the transfer function of the system is the rational function $X(z) = \sum_{i=1}^{K} \frac{z}{z-\gamma_i}$ with poles γ_i.

- The above analysis yields the following properties regarding the ROC:

PROPERTY:

If $x[n]$ is a causal signal, the ROC of its $z-$transform is $|z| > |\gamma_{\max}|$ with $\gamma_{\max}$ the maximum magnitude pole of the $z-$transform.

❑ **In the general case of $x[n]$ being a right-sided signal (RSS) the ROC is as above but might not include ∞ (think why).**

PROPERTY:

No pole can exist in ROC.

ROC: $\sum_n x[n] z^{-n} \neq \pm\infty$

Generic form of a causal signal cont.

(handwritten) bounded: $|\gamma_i| < 1$
ROC: $|z| > |\gamma_i|_{max}$ ($\Rightarrow$) ROC must include the unit circle.

- The signal $x[n] = \sum_{i=1}^{K} \gamma_i^n u[n]$ is bounded only if $|\gamma_i| < 1 \ \forall i$ or $|\gamma_{\max}| < 1$.

- In that case the ROC includes a circle with radius equal to 1. This is known as the **unit circle**.

- The above observation yields the following property:

PROPERTY:

If the ROC of $X(z)$ includes the unit circle in $z-$plane, then the signal in time is bounded and its Discrete Time Fourier Transform exists.

- In case that $\gamma^n u[n]$ is part of a causal system's impulse response, we see that the condition $|\gamma| < 1$ must hold. This is because, since $\lim_{n \to \infty} (\gamma)^n = \infty$, for $|\gamma| > 1$, the system will be unstable in that case.

- Therefore, in causal systems, stability requires that the ROC of the system's transfer function includes the unit circle.

Example: Find the $z-$transform of $x[n] = -\gamma^n u[-n-1]$

- Find the $z-$transform of the anti-causal signal $-\gamma^n u[-n-1]$, where γ is a constant.

- By definition:

$$X[z] = \sum_{n=-\infty}^{\infty} -\gamma^n u[-n-1]z^{-n} = \sum_{n=-\infty}^{-1} -\gamma^n z^{-n} = -\sum_{n=1}^{\infty} \gamma^{-n} z^n = -\sum_{n=1}^{\infty} \left(\frac{z}{\gamma}\right)^n$$

$$= -\frac{z}{\gamma} \sum_{n=0}^{\infty} \left(\frac{z}{\gamma}\right)^n = -\left(\frac{z}{\gamma}\right)\left[1 + \left(\frac{z}{\gamma}\right) + \left(\frac{z}{\gamma}\right)^2 + \left(\frac{z}{\gamma}\right)^3 + \cdots\right]$$

- Therefore,

$$X[z] = -\left(\frac{z}{\gamma}\right)\frac{1}{1-\frac{z}{\gamma}}, \quad \left|\frac{z}{\gamma}\right| < 1$$

$$= \frac{z}{z-\gamma}, \quad |z| < |\gamma|$$

- We notice that the $z-$transform exists for certain values of z, which consist the complement of the ROC of the function $\gamma^n u[n]$ with respect to the $z-$plane.

Generic form of an anti-causal signal

- Consider the anti-causal signal $x[n] = \sum_{i=1}^{K} -\gamma_i^n u[-n-1]$ with $z-$transform $X(z) = \sum_{i=1}^{K} \frac{z}{z-\gamma_i}$.

- In that case the ROC is the intersection of the sets $|z| < |\gamma_i|$, i.e., ROC: $|z| < |\gamma_{\min}|$

- In case that $x[n]$ is the impulse response of a system, the transfer function of the system is the rational function $X(z) = \sum_{i=1}^{K} \frac{z}{z-\gamma_i}$ with poles γ_i.

- The above analysis yield the following property regarding ROCs:

PROPERTY:

If $x[n]$ is an anti-causal signal, the ROC of its $z-$transform is $|z| < |\gamma_{\min}|$ with $\gamma_{\min}$ the minimum magnitude pole of the $z-$transform.

❑ **In the general case of $x[n]$ being a left-sided signal (LSS) the ROC is as above but might not include 0 (think why).**

- We proved that the following two functions:
  - The causal function $\gamma^n u[n]$ and
  - the anti-causal function $-\gamma^n u[-n-1]$ have:
    - ❖ The same analytical expression for their $z-$transforms.
    - ❖ Complementary ROCs. More specifically, the union of their ROCS forms the entire $z-$plane.

- The above observations verify that the analytical expression alone is not sufficient to define the $z-$transform of a signal. The ROC is also required.

- **Example:** Find the $z-$transform of the two-sided signal:

$$x[n] = 2^n u[n] - 4^n u[-n-1]$$

Based on the previous analysis we have:

$$X[z] = \frac{z}{z-2} + \frac{z}{z-4}, \text{ ROC: } |z| > 2 \cap |z| < 4 \text{ or ROC: } 2 < |z| < 4$$

- **Example:** Find the $z-$transform of the two-sided signal:

$$x[n] = 4^n u[n] - 2^n u[-n-1]$$

Based on the previous analysis we have:

$$X[z] = \frac{z}{z-2} + \frac{z}{z-4}, \text{ ROC: } |z| > 4 \cap |z| < 2 \text{ or ROC: } \emptyset$$

PROPERTY:

If $x[n]$ is two-sided signal then the ROC of its $z-$transform is of the form:

❑ $\gamma_1 < |z| < \gamma_2$ **with $\gamma_1,\ \gamma_2$ poles of the system or**

❑ $\emptyset$

Example: Find the $z-$transform of $\delta[n]$ and $u[n]$

- By definition $\delta[0] = 1$ and $\delta[n] = 0$ for $n \neq 0$.

$$X[z] = \sum_{n=-\infty}^{\infty} \delta[n]z^{-n} = \delta[0]z^{-0} = 1$$

- By definition $u[n] = 1$ for $n \geq 0$.

$$X[z] = \sum_{n=-\infty}^{\infty} u[n]z^{-n} = \sum_{n=0}^{\infty} z^{-n} = \frac{1}{1-\frac{1}{z}}, \left|\frac{1}{z}\right| < 1$$

$$= \frac{z}{z-1}, |z| > 1$$

Example: Find the $z-$transform of $\cos\beta n u[n]$

- We write $\cos\beta n = \frac{1}{2}\left(e^{j\beta n} + e^{-j\beta n}\right)$.

- From previous analysis we showed that:

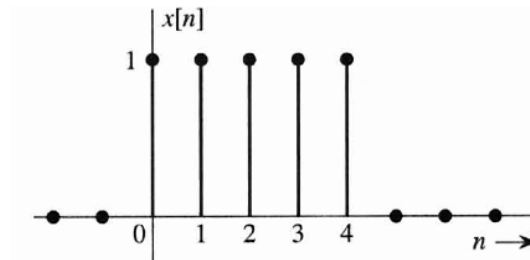$$\gamma^n u[n] \Leftrightarrow \frac{z}{z-\gamma}, \ |z| > |\gamma|$$

- Hence,

$$e^{\pm j\beta n} u[n] \Leftrightarrow \frac{z}{z-e^{\pm j\beta}}, \ |z| > \left|e^{\pm j\beta}\right| = 1$$

- Therefore,

$$X[z] = \frac{1}{2}\left[\frac{z}{z-e^{j\beta}} + \frac{z}{z-e^{-j\beta}}\right] = \frac{z(z-\cos\beta)}{z^2 - 2z\cos\beta + 1}, \ |z| > 1$$

- Find the $z-$transform of the signal depicted in the figure.

- By definition:

$$X[z] = 1 + \frac{1}{z} + \frac{1}{z^2} + \frac{1}{z^3} + \frac{1}{z^4} = \sum_{k=0}^{4}(z^{-1})^k = \frac{1-(z^{-1})^5}{1-z^{-1}} = \frac{z}{z-1}(1-z^{-5})$$

- As with other transforms, inverse $z-$transform is used to derive $x[n]$ from $X[z]$, and is formally defined as:

$$x[n] = \frac{1}{2\pi j} \oint X[z] z^{n-1} dz$$

- Here the symbol $\oint$ indicates an integration in counter-clockwise direction around a circle within the ROC and $z = Re^{j\theta}$.

- Such contour integral is difficult to evaluate (but could be done using Cauchy's residue theorem), therefore we often use other techniques to obtain the inverse $z-$transform.

- One such technique is to use a $z-$transform pairs Table shown in the last two slides with partial fraction expansion.

Proof:

$$\frac{1}{2\pi j}\oint X[z]z^{n-1}dz = \frac{1}{2\pi j}\oint\left(\sum_{m=-\infty}^{\infty} x[m]z^{-m}\right)z^{n-1}dz$$

$$= \sum_{m=-\infty}^{\infty} x[m]\frac{1}{2\pi j}\oint z^{n-m-1}dz = \sum_{m=-\infty}^{\infty} x[m]\,\delta[n-m] = x[n]$$

❑ For the above we used the Cauchy's theorem:

$\frac{1}{2\pi j}\oint z^{k-1}dz = \delta[k]$ for $z = Re^{j\theta}$ anti-clockwise.

$\frac{dz}{d\theta} = jRe^{j\theta} \Rightarrow \frac{1}{2\pi j}\oint z^{k-1}dz = \frac{1}{2\pi j}\int_{\theta=0}^{2\pi} R^{k-1}e^{j(k-1)\theta}\,jRe^{j\theta}\,d\theta =$

$\frac{R^k}{2\pi}\int_{\theta=0}^{2\pi} e^{jk\theta}\,d\theta = R^k\,\delta[k]$

$[\frac{R^k}{2\pi}\int_{\theta=0}^{2\pi} e^{jk\theta}\,d\theta = \begin{cases} 0 & k \neq 0 \\ \frac{R^k}{2\pi}2\pi = R^k & k = 0 \end{cases}]$

- Find the inverse $z-$transform of $X[z] = \frac{8z-19}{(z-2)(Z-3)}$

Solution

$$\frac{X[z]}{z} = \frac{8z-19}{z(z-2)(Z-3)} = \frac{(-\frac{19}{6})}{z} + \frac{3/2}{z-2} + \frac{5/3}{z-3}$$

$$X[z] = -\frac{19}{6} + \frac{3}{2}\left(\frac{z}{z-2}\right) + \frac{5}{3}\left(\frac{z}{z-3}\right)$$

By using the simple transforms that we derived previously we get:

$$x[n] = -\frac{19}{6}\delta[n] + \left[\frac{3}{2}2^n + \frac{5}{3}3^n\right]u[n]$$

- Find the inverse $z-$transform of $X[z] = \dfrac{z(2z^2-11z+12)}{(z-1)(z-2)^3}$

Solution

$$\frac{X[z]}{z} = \frac{(2z^2-11z+12)}{(z-1)(z-2)^3} = \frac{k}{z-1} + \frac{a_0}{(z-2)^3} + \frac{a_1}{(z-2)^2} + \frac{a_2}{(z-2)}$$

- We use the so called **<u>covering method</u>** to find k and a_0

$$k = \left.\frac{(2z^2-11z+12)}{(z-1)(z-2)^3}\right|_{z=1} = -3$$

$$a_0 = \left.\frac{(2z^2-11z+12)}{(z-1)(z-2)^3}\right|_{z=2} = -2$$

The shaded areas above indicate that they are excluded from the entire function when the specific value of z is applied.

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Find the inverse $z-$transform in the case of real repeated poles cont.

- Find the inverse $z-$transform of $X[z] = \dfrac{z(2z^2-11z+12)}{(z-1)(z-2)^3}$

  Solution

$$\frac{X[z]}{z} = \frac{(2z^2-11z+12)}{(z-1)(z-2)^3} = \frac{-3}{z-1} + \frac{-2}{(z-2)^3} + \frac{a_1}{(z-2)^2} + \frac{a_2}{(z-2)}$$

- To find a_2 we multiply both sides of the above equation with z and let $z \to \infty$.

$$0 = -3 - 0 + 0 + a_2 \Rightarrow a_2 = 3$$

- To find a_1 let $z \to 0$.

$$\frac{12}{8} = 3 + \frac{1}{4} + \frac{a_1}{4} - \frac{3}{2} \Rightarrow a_1 = -1$$

$$\frac{X[z]}{z} = \frac{(2z^2-11z+12)}{(z-1)(z-2)^3} = \frac{-3}{z-1} - \frac{2}{(z-2)^3} - \frac{1}{(z-2)^2} + \frac{3}{(z-2)} \Rightarrow$$

$$X[z] = \frac{-3z}{z-1} - \frac{2z}{(z-2)^3} - \frac{z}{(z-2)^2} + \frac{3z}{(z-2)}$$

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Find the inverse $z-$transform in the case of real repeated poles cont.

$$X[z] = \frac{-3z}{z-1} - \frac{2z}{(z-2)^3} - \frac{z}{(z-2)^2} + \frac{3z}{(z-2)}$$

- We use the following properties:

  - $\gamma^n u[n] \Leftrightarrow \dfrac{z}{z-\gamma}$

  - $\dfrac{n(n-1)(n-2)\ldots(n-m+1)}{\gamma^m m!} \gamma^n u[n] \Leftrightarrow \dfrac{z}{(z-\gamma)^{m+1}}$

$[-\dfrac{2z}{(z-2)^3} = (-2)\dfrac{z}{(z-2)^{2+1}} \Leftrightarrow (-2)\dfrac{n(n-1)}{2^2 2!} \gamma^n u[n] = -2\dfrac{n(n-1)}{8} \cdot 2^n u[n]$

- Therefore,

$$x[n] = [-3 \cdot 1^n - 2\frac{n(n-1)}{8} \cdot 2^n - \frac{n}{2} \cdot 2^n + 3 \cdot 2^n]u[n]$$

$$= -\left[3 + \frac{1}{4}(n^2 + n - 12)2^n\right]u[n]$$

Find the inverse z −transform in the case of complex poles

- Find the inverse z −transform of $X[z] = \dfrac{2z(3z+17)}{(z-1)(z^2-6z+25)}$

Solution

$$X[z] = \frac{2z(3z + 17)}{(z - 1)(z - 3 - j4)(z - 3 + j4)}$$

$$\frac{X[z]}{z} = \frac{(2z^2-11z+12)}{(z-1)(z-2)^3} = \frac{k}{z-1} + \frac{a_0}{(z-2)^3} + \frac{a_1}{(z-2)^2} + \frac{a_2}{(z-2)}$$

Whenever we encounter a complex pole we need to use a special partial fraction method called **quadratic factors method**.

$$\frac{X[z]}{z} = \frac{2(3z+17)}{(z-1)(z^2-6z+25)} = \frac{2}{z-1} + \frac{Az+B}{z^2-6z+25}$$

We multiply both sides with z and let $z \to \infty$:

$$0 = 2 + A \Rightarrow A = -2$$

Therefore,

$$\frac{2(3z+17)}{(z-1)(z^2-6z+25)} = \frac{2}{z-1} + \frac{-2z+B}{z^2-6z+25}$$

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Find the inverse $z-$transform in the case of complex poles cont.

$$\frac{2(3z+17)}{(z-1)(z^2-6z+25)} = \frac{2}{z-1} + \frac{-2z+B}{z^2-6z+25}$$

To find B we let $z=0$:

$$\frac{-34}{25} = -2 + \frac{B}{25} \Rightarrow B = 16$$

$$\frac{X[z]}{z} = \frac{2}{z-1} + \frac{-2z+16}{z^2-6z+25} \Rightarrow X[z] = \frac{2z}{z-1} + \frac{z(-2z+16)}{z^2-6z+25}$$

- We use the following property:

$$r|\gamma|^n \cos(\beta n + \theta)\, u[n] \Leftrightarrow \frac{z(Az+B)}{z^2+2az+|\gamma|^2} \text{ with } A = -2, B = 16, a = -3, |\gamma| = 5.$$

$$r = \sqrt{\frac{A^2|\gamma|^2+B^2-2AaB}{|\gamma|^2-a^2}} = \sqrt{\frac{4\cdot25+256-2\cdot(-2)\cdot(-3)\cdot16}{25-9}} = 3.2, \beta = \cos^{-1}\frac{-a}{|\gamma|} = 0.927 rad,$$

$$\theta = \tan^{-1}\frac{Aa-B}{A\sqrt{|\gamma|^2-a^2}} = -2.246 rad.$$

Therefore, $x[n] = [2 + 3.2\cos(0.927n - 2.246)]u[n]$

$z-$transform Table

No.	$x[n]$	$X[z]$
1	$\delta[n-n]$	z^{-k}
2	$u[n]$	$\dfrac{z}{z-1}$
3	$nu[n]$	$\dfrac{z}{(z-1)^2}$
4	$n^2u[n]$	$\dfrac{z(z+1)}{(z-1)^3}$
5	$n^3u[n]$	$\dfrac{z(z^2+4z+1)}{(z-1)^4}$
6	$\gamma^n u[n]$	$\dfrac{z}{z-\gamma}$
7	$\gamma^{n-1}u[n-1]$	$\dfrac{1}{z-\gamma}$
8	$n\gamma^n u[n]$	$\dfrac{\gamma z}{(z-\gamma)^2}$

z —transform Table

No.	$x[n]$	$X[z]$
10	$\dfrac{n(n-1)(n-2)\cdots(n-m+1)}{\gamma^m m!}\gamma^n u[n]$	$\dfrac{z}{(z-\gamma)^{m+1}}$
11a	$|\gamma|^n \cos \beta n\, u[n]$	$\dfrac{z(z-|\gamma|\cos\beta)}{z^2-(2|\gamma|\cos\beta)z+|\gamma|^2}$
11b	$|\gamma|^n \sin \beta n\, u[n]$	$\dfrac{z|\gamma|\sin\beta}{z^2-(2|\gamma|\cos\beta)z+|\gamma|^2}$
12a	$r|\gamma|^n \cos(\beta n+\theta)u[n]$	$\dfrac{rz[z\cos\theta-|\gamma|\cos(\beta-\theta)]}{z^2-(2|\gamma|\cos\beta)z+|\gamma|^2}$
12b	$r|\gamma|^n \cos(\beta n+\theta)u[n] \qquad \gamma=|\gamma|e^{j\beta}$	$\dfrac{(0.5re^{j\theta})z}{z-\gamma}+\dfrac{(0.5re^{-j\theta})z}{z-\gamma^*}$
12c	$r|\gamma|^n \cos(\beta n+\theta)u[n]$	$\dfrac{z(Az+B)}{z^2+2az+|\gamma|^2}$

$$r=\sqrt{\dfrac{A^2|\gamma|^2+B^2-2AaB}{|\gamma|^2-a^2}} \qquad \beta=\cos^{-1}\dfrac{-a}{|\gamma|} \qquad \theta=\tan^{-1}\dfrac{Aa-B}{A\sqrt{|\gamma|^2-a^2}}$$