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$$\left[ \hat{a}_{\mathbf{x}}(\frac{1}{\partial}1_{\mathbf{z}})\{\partial \mathbf{y}\} - \{\frac{1}{\partial}1_{\mathbf{y}}\}\{\partial \mathbf{z}\} - \hat{a}_{\mathbf{y}}(\frac{1}{\partial}1_{\mathbf{z}})\{\partial \mathbf{x}\} - \{\frac{1}{\partial}1_{\mathbf{x}}\}\{\partial \mathbf{z}\} + \hat{a}_{\mathbf{z}}(\frac{1}{\partial}1_{\mathbf{y}})\{\partial \mathbf{x}\} - \{\frac{1}{\partial}1_{\mathbf{x}}\}\{\partial \mathbf{y}\} \right]$$

# ECE 6310 - Advanced Electromagnetic Fields: Homework Set #2

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## 1 Preliminaries

In this document, we use standard notation for electromagnetic theory. Key equations and concepts are summarized below:

### Vector Notation

- $\mathcal{E}$ : Electric field intensity
- $\mathcal{H}$ : Magnetic field intensity
- $\mathcal{D}$ : Electric flux density
- $\mathcal{B}$ : Magnetic flux density
- $\mathcal{J}$ : Current density
- $\rho_v$ : Volume charge density

### Differential Operators

- $\nabla \cdot$  : Divergence of a vector field
- $\nabla \times$  : Curl of a vector field
- $\nabla$  : Gradient of a scalar field
- $\partial_i$  : Partial derivative with respect to the independent basis element  $i$

## Maxwell's Equations

In integral form, Maxwell's equations are given by:

$$\oint_{\partial V} \mathcal{E} \cdot d\mathbf{\hat{\downarrow}} = -\frac{d}{dt} \int_V \mathcal{B} \cdot d\mathcal{S} \quad (\text{Faraday's Law of Induction}) \quad (1)$$

$$\oint_{\partial V} \mathcal{H} \cdot d\mathbf{\hat{\downarrow}} = \int_V \mathcal{J} \cdot d\mathcal{S} + \frac{d}{dt} \int_V \mathcal{D} \cdot d\mathcal{S} \quad (\text{Ampère's Circuital Law}) \quad (2)$$

$$\int_V \mathcal{D} \cdot d\mathcal{S} = \int_V \rho_v dV \quad (\text{Gauss's Law for Electricity}) \quad (3)$$

$$\int_V \mathcal{B} \cdot d\mathcal{S} = 0 \quad (\text{Gauss's Law for Magnetism}) \quad (4)$$

## Other Relevant Equations

- Continuity Equation:  $\nabla \cdot \mathcal{J} + \partial_t \rho_v = 0$
- Relationship between  $\mathcal{E}$ ,  $\mathcal{D}$ :  $\mathcal{D} = \epsilon \mathcal{E}$
- Relationship between  $\mathcal{H}$ ,  $\mathcal{B}$ :  $\mathcal{B} = \mu \mathcal{H}$

## Boundary Conditions

Discuss the boundary conditions for  $\mathcal{E}$ ,  $\mathcal{H}$ ,  $\mathcal{D}$ , and  $\mathcal{B}$  at interfaces between different media.

### Problem 3.2

Verify that (3-28a) and (3-28b) are solutions to (3-26a)

To solve this problem, we can first set up the expressions we need

(3-26a)

$$\frac{d^2 f}{dx^2} = -\beta_x^2 f \quad (5)$$

(3-28a)

$$\begin{aligned} f(x) &= A_1 e^{-j\beta_x x} + B_1 e^{j\beta_x x} \\ \frac{d}{dx} f(x) &= -j\beta_x A_1 e^{-j\beta_x x} + j\beta_x B_1 e^{j\beta_x x} \\ \frac{d^2}{dx^2} f(x) &= (-j\beta_x)^2 A_1 e^{-j\beta_x x} + (j\beta_x)^2 B_1 e^{j\beta_x x} \\ \frac{d^2}{dx^2} f(x) &= -\beta_x^2 A_1 e^{-j\beta_x x} - \beta_x^2 B_1 e^{j\beta_x x} \\ &= -\beta_x^2 (A_1 e^{-j\beta_x x} + B_1 e^{j\beta_x x}) \\ &= -\beta_x^2 f(x) \end{aligned}$$

(3-28b)

$$\begin{aligned} f(x) &= C_1 \cos(\beta_x x) + D_1 \sin(\beta_x x) \\ \frac{d}{dx} f(x) &= -\beta_x C_1 \sin(\beta_x x) + \beta_x D_1 \cos(\beta_x x) \\ \frac{d^2}{dx^2} f(x) &= -\beta_x^2 C_1 \cos(\beta_x x) - \beta_x^2 D_1 \sin(\beta_x x) \\ &= -\beta_x^2 (C_1 \cos(\beta_x x) + D_1 \sin(\beta_x x)) \\ &= -\beta_x^2 f(x) \end{aligned}$$

### Problem 4.2

Using Maxwell's equations, find the magnetic field components for the wave whose electric field is given in Example 4-1. Compare your answer with that obtained in the solution of Example 4-1.

The expression for the magnetic field in terms of the electric field is:

$$H = -\frac{1}{j\omega\mu} \{$$

Example 4-1 shows the electric field as:

$$E = \hat{a}_y(E_0^+ e^{-j\beta z} + E_0^- e^{+j\beta z}) = \hat{a}_y(E_y^+ + E_y^-)$$

Since it only has a  $y$  component, we can take all the parts that do not have a  $y$  component and set them to 0.

$$\begin{aligned} H &= -\frac{1}{j\omega\mu} \left[ \hat{a}_x \left( \frac{\partial E_z}{\partial y} - \frac{\partial E_y}{\partial z} \right) - \hat{a}_y \left( \frac{\partial E_z}{\partial x} - \frac{\partial E_x}{\partial z} \right) + \hat{a}_z \right. \\ &= -\frac{1}{j\omega\mu} \left[ -\hat{a}_x \frac{\partial E_y}{\partial z} + \hat{a}_z \frac{\partial E_y}{\partial x} \right] \end{aligned}$$

We can also get rid of the partial w.r.t.  $x$  since  $E$  does not have a dependence on  $x$ .

$$\begin{aligned} H &= -\frac{1}{j\omega\mu} \left[ -\hat{a}_x \frac{\partial E_y}{\partial z} + \hat{a}_z \frac{\partial E_y}{\partial x} \right] \\ H &= \frac{1}{j\omega\mu} \left[ \hat{a}_x \frac{\partial E_y}{\partial z} \right] \\ H &= \frac{1}{j\omega\mu} \left[ \hat{a}_x \frac{\partial}{\partial z} (E_y^+ + E_y^-) \right] \\ H &= \frac{1}{j\omega\mu} \left[ \hat{a}_x (-j\beta E_0^+ e^{-j\beta z} + j\beta E_0^- e^{+j\beta z}) \right] \\ H &= \frac{\beta}{\omega\mu} \left[ \hat{a}_x (E_0^+ e^{-j\beta z} - E_0^- e^{+j\beta z}) \right] \end{aligned}$$

Given the result here, we can infer that:

$$\begin{aligned} \eta &= \frac{\omega\mu}{\beta} = \frac{\omega\mu}{\omega\sqrt{\mu\epsilon}} = \sqrt{\frac{\mu^2}{\mu\epsilon}} \\ &= \sqrt{\frac{\mu}{\epsilon}} \end{aligned}$$

which is the expected impedance of free space.

## Problem 4.22

Sea water is an important medium in communication between submerged submarines or between submerged submarines and receiving and transmitting stations located above the surface of the sea. Assuming the constitutive

electrical parameters of the sea are  $\sigma = 4\frac{S}{m}$ ,  $\epsilon_r = 81$ ,  $\mu_r = 1$ , and  $f = 104Hz$ , find the following:

Before we start, it would be good to get the following value to start:

$$\begin{aligned}\left(\frac{\sigma}{\omega\epsilon}\right)^2 &= \left(\frac{4}{208\pi \cdot 10^4 \cdot 81 \cdot 8.854} \cdot 10^{12}\right)^2 \\ &= \left(\frac{4}{208\pi \cdot 81 \cdot 8.854} \cdot 10^8\right)^2 \\ &= 7.285e^5 \gg 1\end{aligned}$$

Given this result, we can take the parameters of the sea to be a good conductor. As such,  $\alpha \approx \beta$ .

(a) Complex propagation constant  $\gamma\frac{1}{m}$ .

$$\begin{aligned}\gamma &= \alpha + j\beta = \sqrt{\frac{\omega\mu\sigma}{2}}(1 + j) \\ &= 0.3974(1 + j)\end{aligned}$$

(b) Phase velocity  $v\frac{m}{s}$ .

$$\begin{aligned}v &= \frac{\omega}{\beta} = \frac{\omega}{\sqrt{\frac{\omega\mu\sigma}{2}}} \\ &= \sqrt{\frac{2\omega^2}{\omega\mu\sigma}} = \sqrt{\frac{2\omega}{\mu\sigma}} \\ &= 1.581e^5 \left[\frac{m}{s}\right]\end{aligned}$$

(c) Wavelength  $\lambda [m]$ .

$$\begin{aligned}\lambda &= \frac{2\pi}{\beta} = 2\pi\sqrt{\frac{2}{\omega\mu\sigma}} \\ &= \sqrt{\frac{8\pi^2}{2\pi f\mu\sigma}} = \sqrt{\frac{4\pi}{f\mu\sigma}} \\ &= 15.81[m]\end{aligned}$$

(d) Attenuation constant  $\alpha\frac{N}{m}$ .

$$\begin{aligned}\alpha &= \sqrt{\frac{\omega\mu\sigma}{2}} = \sqrt{\pi f\mu\sigma} \\ &= 0.3974 \left[\frac{N}{m}\right]\end{aligned}$$

(e) Skin depth  $\delta$  [m].

$$\begin{aligned}\delta &= \frac{1}{\alpha} = \sqrt{\frac{2}{\omega\mu\sigma}} \\ &= \frac{1}{0.3974} = 2.52 \text{ [m]}\end{aligned}$$

## Problem 4.26

In a source-free, free-space region, the complex magnetic field of a time-harmonic field is represented by:

$$H = \left[ \hat{a}_x(1+j) + \hat{a}_z \left( \sqrt{2}e^{-j\frac{\pi}{4}} \right) \right] \frac{E_0}{\eta_0} e^{-j\beta_0 y}$$

where  $E_0$  is a constant and  $\eta_0$  is the intrinsic impedance of free space. Determine the:

(a) Polarization of the wave (linear, circular, or elliptical). Justify your answer.

Since the  $z$  component of  $H$  has a quarter  $\pi$  rotation advancement, we can replace the quarter rotation using Eulers equation. A quarter turn is one of the simpler ones to replace since the real and imaginary components are both  $\frac{\sqrt{2}}{2}$ .

$$\begin{aligned}e^{-j\frac{\pi}{4}} &= \cos\left(\frac{\pi}{4}\right) + j\sin\left(\frac{\pi}{4}\right) \\ &= \frac{\sqrt{2}}{2} + j\frac{\sqrt{2}}{2} = \frac{\sqrt{2}}{2}(1+j) \\ H &= \left[ \hat{a}_x(1+j) + \hat{a}_z \left( \sqrt{2} \left( \frac{\sqrt{2}}{2}(1+j) \right) \right) \right] \frac{E_0}{\eta_0} e^{-j\beta_0 y} \\ H &= [\hat{a}_x(1+j) + \hat{a}_z(1+j)] \frac{E_0}{\eta_0} e^{-j\beta_0 y}\end{aligned}$$

$$H = [\hat{a}_x + \hat{a}_z] (1+j) \frac{E_0}{\eta_0} e^{-j\beta_0 y}$$

Since the vector contains components that are equivalent in their behavior, the polarization of the wave is linear.

(b) Sense of rotation, if any.

No sense of rotation since the polarization is linear.

(c) Corresponding electric field.

$$\begin{aligned} E &= -\eta_0 \hat{k} \times H \\ &= -\eta_0 [aH] \end{aligned}$$

Since we have the  $y$  direction as the propagation direction, we can replace the first and third components of  $\hat{a}$  with 0.

$$\begin{aligned} &= -\eta_0 [\hat{a}_x (1 \cdot H_3 - 0 \cdot H_2) - \hat{a}_y (0 \cdot H_3 - 0 \cdot H_1) + \hat{a}_z (0 \cdot H_2 - 1 \cdot H_1)] \\ &= -\eta_0 [\hat{a}_x H_3 - \hat{a}_z H_1] \\ H_1 &= H_3 \\ \therefore E &= -\eta_0 [\hat{a}_x - \hat{a}_z] (1 + j) \frac{E_0}{\eta_0} e^{-j\beta_0 y} \\ &= -E_0 [\hat{a}_x - \hat{a}_z] (1 + j) e^{-j\beta_0 y} \end{aligned}$$

## Problem 5.4

A vertical interface is formed by having free space to its left and a lossless dielectric medium to its right with  $\epsilon = 4\epsilon_0$  and  $\mu = \mu_0$ , as shown in Figure P5-4. The incident electric field of a uniform plane wave traveling in the free-space medium and incident normally upon the interface has a value of  $2 \cdot 10^3 \frac{V}{m}$  right before it strikes the boundary. At a frequency of  $3GHz$ , find the:

```
[scale=1.5, axis/.style=-->, >=stealth']
[gray!40] (0,-1.5) -- (1.5,-1.5) -- (1.5,1.5) -- (0,1.5) -- cycle; [axis] (0,0) -- (2,0)
node(xline)[right] z; [axis] (0,0) -- (0,2) node(yline)[above] x;
(0,0) circle (3.5pt); [black] (0,0) circle (1.75pt);
at (-0.5,1)  $\epsilon_0, \mu_0$ ; at (1,1)  $4\epsilon_0, \mu_0$ ;
[axis] (0,0) -- (0,-1.5) node(yline)[below] y;
at (0.5,-2.5) Figure P5-4;
```

(a) Reflection coefficient.



$$\begin{aligned}
\eta &= \sqrt{\frac{\mu}{\epsilon}} \\
\eta_1 &= \sqrt{\frac{\mu_0}{\epsilon_0}} = \eta_0 \\
\eta_2 &= \sqrt{\frac{\mu_2}{\epsilon_2} \frac{\mu_0}{4\epsilon_0}} = \frac{1}{2}\eta_0 \\
\Gamma &= \frac{\eta_2 - \eta_1}{\eta_2 + \eta_1} = \frac{.5 - 1}{.5 + 1} = -\frac{1}{3}
\end{aligned}$$

(b) SWR in the free-space medium.

$$\begin{aligned}
swr &= \frac{1 + |\Gamma|}{1 - |\Gamma|} \\
&= \frac{1 + .333\dots}{1 - .333\dots} = \frac{\frac{4}{3}}{\frac{2}{3}} \\
&= \frac{4}{2} = 2
\end{aligned}$$

(c) Positions (in meters) in the free-space medium where the electric field maxima and minima occur.

$$|\mathbf{E}^{tot}| = E_0(e^{-j\beta z} + \Gamma e^{j\beta z})$$

(d) Max and min values of the electric field in the free-space medium.

## Problem 5.9

A uniform plane wave traveling in air is incident normally on a half space occupied by a lossless dielectric medium of relative permittivity of 4. The reflections can be eliminated by placing another dielectric slab,  $\frac{\lambda}{4}$  thick, between the air and the original dielectric medium, as shown in Figure P5-9. To accomplish this, the intrinsic impedance  $\eta_1$  of the slab must be equal to  $\sqrt{\eta_0\eta_2}$  where  $\eta_0$  and  $\eta_2$  are, respectively, the intrinsic impedances of air and the original dielectric medium. Assuming that the relative permeabilities of all the media are unity, what should the relative permittivity of the dielectric slab be to accomplish this?

```

[scale=1.5, axis/.style=->, >=stealth']
[gray!40] (0,-1.5) -- (1.5,-1.5) -- (1.5,1.5) -- (0,1.5) -- cycle; [gray!60] (1,-1.5) --
(2,-1.5) -- (2,1.5) -- (1,1.5) -- cycle; [axis] (-.5,0) -- (2.75,0) node(xline)[right]
; [axis] (0,0) -- (0,2) node(yline)[above] ; [axis] (0,.5) -- (1,.5) node(yline)]] ;
at (.5,.7)  $\frac{\lambda_1}{4}$ ;
(0,0) circle (3.5pt); [black] (0,0) circle (1.75pt);
at (-0.5,1.25)  $\eta_0$ ; at (.5,1.25)  $\eta_1$ ; at (.5,-.5)  $\epsilon_{r1} = ?$ ; at (1.5,1.25)  $\eta_2$ ; at
(1.5,-.5)  $\epsilon_{r2} = 4$ ;
[axis] (0,0) -- (0,-2) node(yline)[below] ;
at (0.5,-2.5) Figure P5-9;

```

This problem is a simple one. First we set the expressions for each of the impedances using the equation from [1]:

$$\eta_0 = \sqrt{\frac{\mu_0}{\epsilon_0}}$$

$$\eta_1 = \sqrt{\frac{\mu_{r1}\mu_0}{\epsilon_{r1}\epsilon_0}} = \sqrt{\frac{\mu_{r1}}{\epsilon_{r1}}} \eta_0$$

$$\eta_2 = \sqrt{\frac{\mu_{r2}\mu_0}{\epsilon_{r2}\epsilon_0}} = \sqrt{\frac{\mu_{r2}}{\epsilon_{r2}}} \eta_0$$

Plugging in the values for what we know:

$$\eta_2 = \sqrt{\frac{1}{4}} \eta_0 = \frac{1}{2} \eta_0$$

$$\eta_1 = \sqrt{\frac{\mu_{r1}}{\epsilon_{r1}}} \eta_0 = \sqrt{\eta_0 \eta_2} = \sqrt{\frac{1}{2} \eta_0^2} = \sqrt{\frac{1}{2}} \eta_0$$

Now we set the expression for  $\eta_1$  equal to the expression we have, and solve for the permittivity:

$$\eta_1 = \sqrt{\frac{\mu_{r1}}{\epsilon_{r1}}} \eta_0 = \sqrt{\frac{1}{2}} \eta_0$$

$$\therefore \sqrt{\frac{\mu_{r1}}{\epsilon_{r1}}} = \sqrt{\frac{1}{2}}$$

If we have  $\mu_{r1} = 1$  then we can say that the relative permittivity of the middle slab should be 2.

## Problem 5.21

A uniform plane wave traveling in a lossless dielectric is incident normally on a flat interface formed by the presence of air. For  $\epsilon_r$  's of 2.56, 4, 9, 16, 25, and 81:

- (a) Determine the critical angles.

$$\theta_i \geq \theta_c = \sin^{-1} \left( \sqrt{\frac{\mu_2 \epsilon_2}{\mu_1 \epsilon_1}} \right)$$

- (b) Find the Brewster angles if the wave is of parallel polarization.

$$\theta_B = \tan^{-1} \left( \sqrt{\frac{\epsilon_2}{\epsilon_1}} \right)$$

$$\theta_B = \cos^{-1} \left( \sqrt{\frac{\epsilon_1}{\epsilon_1 + \epsilon_2}} \right)$$

$$\theta_B = \sin^{-1} \left( \sqrt{\frac{\epsilon_2}{\epsilon_1 + \epsilon_2}} \right)$$

- (c) Compare the critical and Brewster angles found in parts (a) and (b).  
(d) Plot the magnitudes of the reflection coefficients for both perpendicular,  $|\Gamma_{\perp}|$ , and parallel,  $|\Gamma_{\parallel}|$ , polarizations versus incidence angle.  
(e) Plot the phase (in degrees) of the reflection coefficients for both perpendicular and parallel polarizations versus incidence angle.

## References

- [1] Constantine A. Balanis. *advanced engineering electromagnetics*, chapter 1, page 2–3. John Wiley & Sons, 2024.