



LMR14020 SIMPLE SWITCHER® 40V 2A、2.2MHz 降压转换器，具有 40μA I_Q

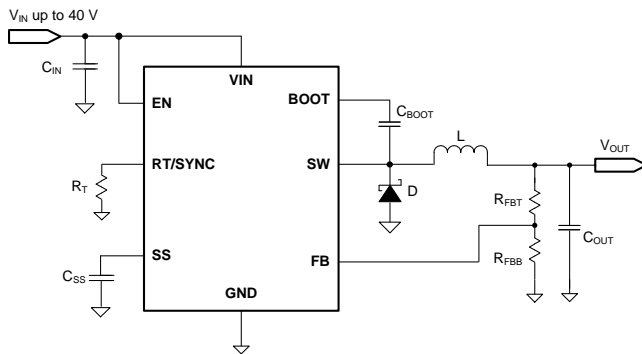
1 特性

- 输入电压范围：4V 至 40V
- 2A 持续输出电流
- 40μA 超低工作静态电流
- 90mΩ 高侧金属氧化物半导体场效应晶体 (MOSFET)
- 最短导通时间：75ns
- 电流模式控制
- 可调节开关频率范围：200kHz 至 2.5MHz
- 与外部时钟频率同步
- 内部补偿方便使用
- 支持高占空比运行
- 精密使能引脚
- 关断电流：1μA
- 外部软启动
- 热保护、过压保护和短路保护
- 8 引脚 HSOIC PowerPAD™ 封装

2 应用范围

- 汽车电池稳压
- 工业用电源
- 电信和数据通信系统
- 电池供电系统

4 简化电路原理图



3 说明

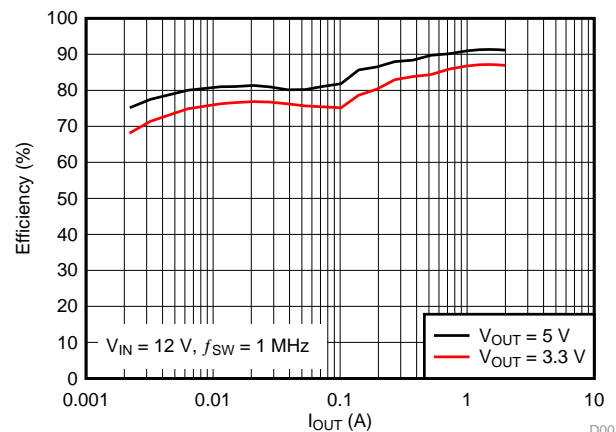
LMR14020 器件是一款具有集成型高侧 MOSFET 的 40V、2A 降压稳压器。该器件具有 4V 至 40V 的宽输入电压范围，适用于从工业到汽车各类应用中非稳压电源的电源调节。该稳压器在休眠模式下的静态电流为 40μA，非常适合电池供电类系统。并且在关断模式下具有 1μA 的超低电流，可进一步延长电池使用寿命。该稳压器的可调开关频率范围较宽，这使得效率或外部元件尺寸能够得到优化。内部环路补偿意味着用户不用承担设计环路补偿组件的枯燥工作。并且还能够以最大限度减少器件的外部元件数。精密使能输入简化了稳压器控制和系统电源排序。此外，该器件还内置多种保护特性：逐周期电流限制保护、应对功耗过大的热感测和热关断保护、以及输出过压保护。

器件信息⁽¹⁾

器件型号	封装	封装尺寸（标称值）
LMR14020SDDA	HSOIC-8	4.89mm x 3.90mm

(1) 要了解所有可用封装，请见数据表末尾的可订购产品附录。

效率与输出电流间的关系



D001



目录

1	特性	1	8.1	Overview	8
2	应用范围	1	8.2	Functional Block Diagram	8
3	说明	1	8.3	Feature Description	9
4	简化电路原理图	1	9	Application and Implementation	15
5	修订历史记录	2	9.1	Application Information	15
6	Pin Configuration and Functions	3	9.2	Typical Application	15
7	Specifications	4	10	Power Supply Recommendations	21
7.1	Absolute Maximum Ratings	4	11	Layout	21
7.2	ESD Ratings	4	11.1	Layout Guidelines	21
7.3	Recommended Operating Conditions	4	11.2	Layout Example	22
7.4	Thermal Information	4	12	器件和文档支持	23
7.5	Electrical Characteristics	5	12.1	商标	23
7.6	Switching Characteristics	5	12.2	静电放电警告	23
7.7	Typical Characteristics	6	12.3	术语表	23
8	Detailed Description	8	13	机械封装和可订购信息	23

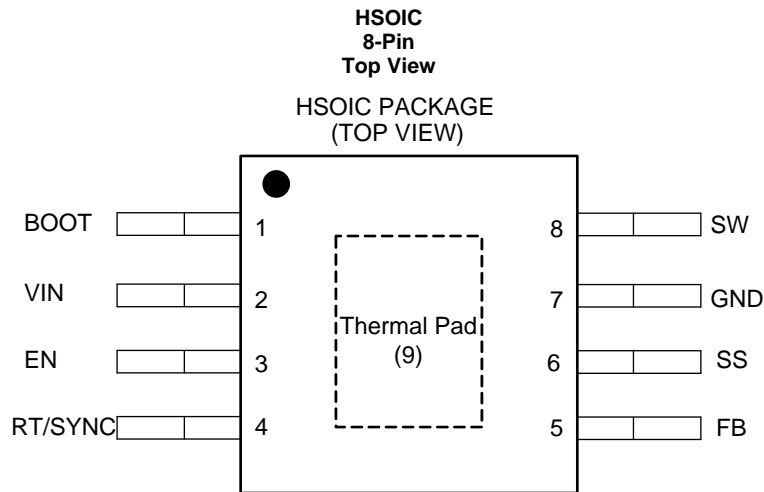
5 修订历史记录

Changes from Original (February 2015) to Revision A

Page

• 已更改 产品预览至量产数据	1
-----------------------	----------

6 Pin Configuration and Functions



Pin Functions

PIN		TYPE ⁽¹⁾	DESCRIPTION
NAME	NO.		
BOOT	1	O	Bootstrap capacitor connection for high-side MOSFET driver. Connect a high quality 0.1 μ F capacitor from BOOT to SW.
VIN	2	I	Connect to power supply and bypass capacitors C_{IN} . Path from VIN pin to high frequency bypass C_{IN} and GND must be as short as possible.
EN	3	I	Enable pin, with internal pull-up current source. Pull below 1.2 V to disable. Float or connect to VIN to enable. Adjust the input under voltage lockout with two resistors. See the Enable and Adjusting Under voltage lockout section.
RT/SYNC	4	I	Resistor Timing or External Clock input. An internal amplifier holds this pin at a fixed voltage when using an external resistor to ground to set the switching frequency. If the pin is pulled above the PLL upper threshold, a mode change occurs and the pin becomes a synchronization input. The internal amplifier is disabled and the pin is a high impedance clock input to the internal PLL. If clocking edges stop, the internal amplifier is re-enabled and the operating mode returns to frequency programming by resistor.
FB	5	I	Feedback input pin, connect to the feedback divider to set V_{OUT} . Do not short this pin to ground during operation.
SS	6	O	Soft-start control pin. Connect to a capacitor to set soft-start time.
GND	7	G	System ground pin.
SW	8	O	Switching output of the regulator. Internally connected to high-side power MOSFET. Connect to power inductor.
Thermal Pad	9	G	Major heat dissipation path of the die. Must be connected to ground plane on PCB.

(1) I = Input, O = Output, G = Ground

7 Specifications

7.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted) ⁽¹⁾

		MIN	MAX	UNIT
Input Voltages	VIN, EN to GND	-0.3	44	V
	BOOT to GND	-0.3	49	
	SS to GND	-0.3	5	
	FB to GND	-0.3	7	
	RT/SYNC to GND	-0.3	3.6	
Output Voltages	BOOT to SW		6.5	V
	SW to GND	-3	44	
T _J	Junction temperature	-40	150	°C
T _{stg}	Storage temperature	-65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

7.2 ESD Ratings

PARAMETER	DEFINITION		VALUE	UNIT
V _(ESD)	Electrostatic discharge	Human body model (HBM) ⁽¹⁾	2	kV
		Charged device model (CDM) ⁽²⁾	0.5	

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.

- (2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

7.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

		MIN	MAX	UNIT
Buck Regulator	VIN	4	40	V
	VOUT	0.8	28	
	BOOT		45	
	SW	-1	40	
	FB	0	5	
Control	EN	0	40	V
	RT/SYNC	0	3.3	
	SS	0	3	
Frequency	Switching frequency range at RT mode	200	2500	kHz
	Switching frequency range at SYNC mode	250	2300	
Temperature	Operating junction temperature, T _J	-40	125	°C

7.4 Thermal Information

THERMAL METRIC ⁽¹⁾		DDA	UNIT
		8 PINS	
R _{θJA}	Junction-to-ambient thermal resistance	42.5	°C/W
Ψ _{JT}	Junction-to-top characterization parameter	9.9	
Ψ _{JB}	Junction-to-board characterization parameter	25.4	
R _{θJC(top)}	Junction-to-case (top) thermal resistance	56.1	
R _{θJC(bot)}	Junction-to-case (bottom) thermal resistance	3.8	
R _{θJB}	Junction-to-board thermal resistance	25.5	

- (1) For more information about traditional and new thermal metrics, see the *IC Package Thermal Metrics* application report, [SPRA953](#).

7.5 Electrical Characteristics

Limits apply over the recommended operating junction temperature (T_J) range of -40°C to $+125^{\circ}\text{C}$, unless otherwise stated. Minimum and Maximum limits are specified through test, design or statistical correlation. Typical values represent the most likely parametric norm at $T_J = 25^{\circ}\text{C}$, and are provided for reference purposes only. Unless otherwise specified, the following conditions apply: $V_{IN} = 4.0\text{ V}$ to 40 V

PARAMETER		TEST CONDITION	MIN	TYP	MAX	UNIT
POWER SUPPLY (VIN PIN)						
V _{IN}	Operation input voltage		4		40	V
UVLO	Under voltage lockout thresholds	Rising threshold	3.5	3.7	3.9	V
		Hysteresis		285		mV
I _{SHDN}	Shutdown supply current	V _{EN} = 0 V, T _A = 25°C, 4.0 V ≤ V _{IN} ≤ 40 V		1.0	3.0	μA
I _Q	Operating quiescent current (non-switching)	V _{FB} = 1.0 V, T _A = 25°C		40		μA
ENABLE (EN PIN)						
V _{EN_TH}	EN Threshold Voltage		1.05	1.20	1.38	V
I _{EN_PIN}	EN PIN current	Enable threshold +50 mV		-4.6		μA
		Enable threshold -50 mV		-1.0		
I _{EN_HYS}	EN hysteresis current			-3.6		μA
EXTERNAL SOFT-START						
I _{SS}	SS pin current	T _A = 25°C		3		μA
VOLTAGE REFERENCE (FB PIN)						
V _{FB}	Feedback voltage	T _J = 25°C	0.744	0.750	0.756	V
		T _J = -40°C to 125°C	0.735	0.750	0.765	V
HIGH-SIDE MOSFET						
R _{DS_ON}	On-resistance	V _{IN} = 12 V, BOOT to SW = 5.8 V		90	180	mΩ
High-side MOSFET CURRENT LIMIT						
I _{LIMIT}	Current limit	V _{IN} = 12 V, T _A = 25°C, Open Loop	2.5	3.2	3.8	A
THERMAL PERFORMANCE						
T _{SHDN}	Thermal shutdown threshold			170		°C
T _{HYS}	Hysteresis			12		

7.6 Switching Characteristics

over operating free-air temperature range (unless otherwise noted)

PARAMETER		TEST CONDITION	MIN	TYP	MAX	UNIT
f_{SW}	Switching frequency	$R_T = 49.9\text{ k}\Omega$, 1% accuracy	400	500	600	kHz
V_{SYNC_HI}	SYNC clock high level threshold		1.7			V
V_{SYNC_LO}	SYNC clock low level threshold				0.5	
T_{SYNC_MIN}	Minimum SYNC input pulse width	Measured at 500 kHz, $V_{SYNC_HI} > 3\text{ V}$, $V_{SYNC_LO} < 0.3\text{ V}$		30		ns
T_{LOCK_IN}	PLL lock in time	Measured at 500 kHz		100		μs
T_{ON_MIN}	Minimum controllable on time	$V_{IN} = 12\text{ V}$, BOOT to SW = 5.8 V, $I_{Load} = 1\text{ A}$		75		ns
D_{MAX}	Maximum duty cycle	$f_{SW} = 200\text{ kHz}$		97		%

7.7 Typical Characteristics

Unless otherwise specified the following conditions apply: $V_{IN} = 12\text{ V}$, $f_{SW} = 1\text{ MHz}$, $L = 5.5\text{ }\mu\text{H}$, $C_{OUT} = 47\text{ }\mu\text{F}$, $T_A = 25^\circ\text{C}$.

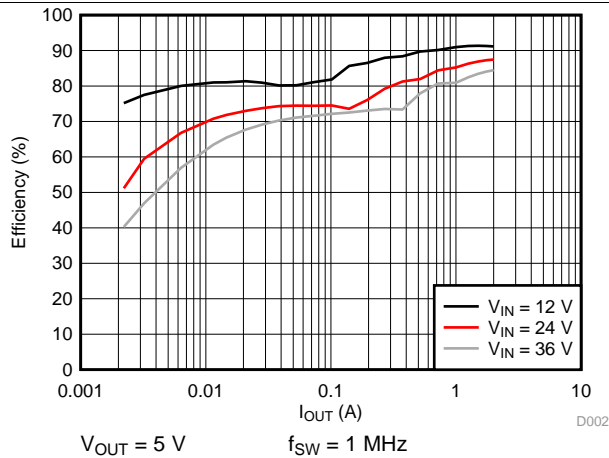


Figure 1. Efficiency vs. Load Current

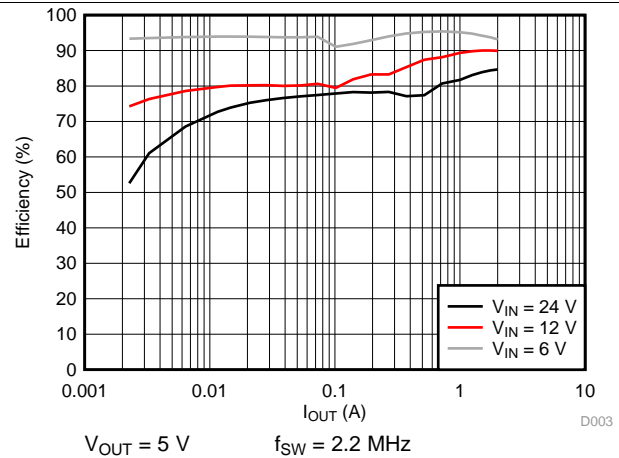


Figure 2. Efficiency vs. Load Current

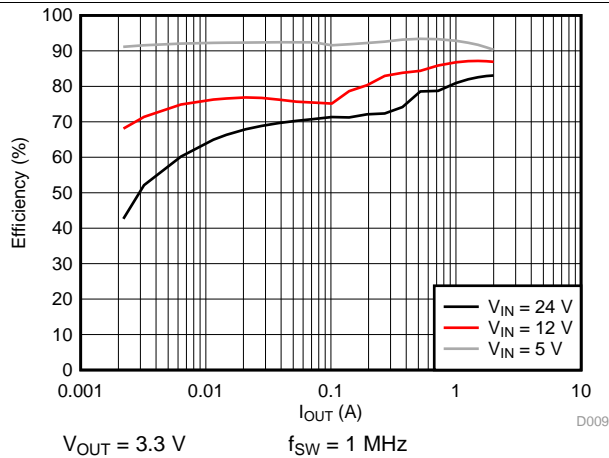


Figure 3. Efficiency vs. Load Current

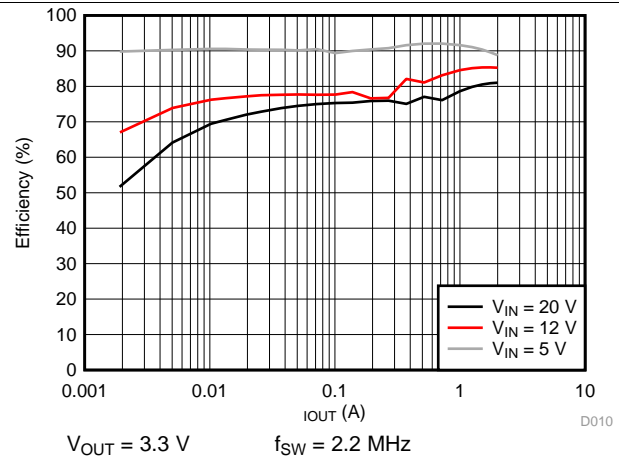


Figure 4. Efficiency vs. Load Current

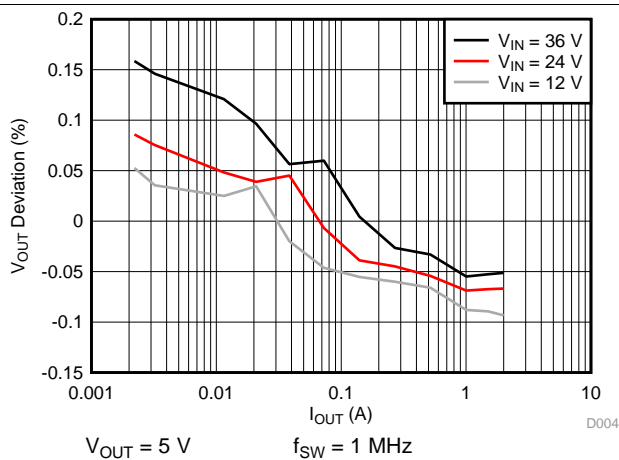


Figure 5. Load Regulation

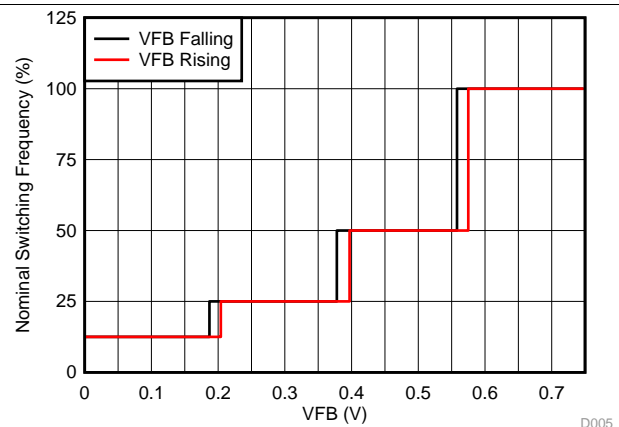


Figure 6. Frequency vs V_{FB}

Typical Characteristics (continued)

Unless otherwise specified the following conditions apply: $V_{IN} = 12\text{ V}$, $f_{SW} = 1\text{ MHz}$, $L = 5.5\text{ }\mu\text{H}$, $C_{OUT} = 47\text{ }\mu\text{F}$, $T_A = 25^\circ\text{C}$.

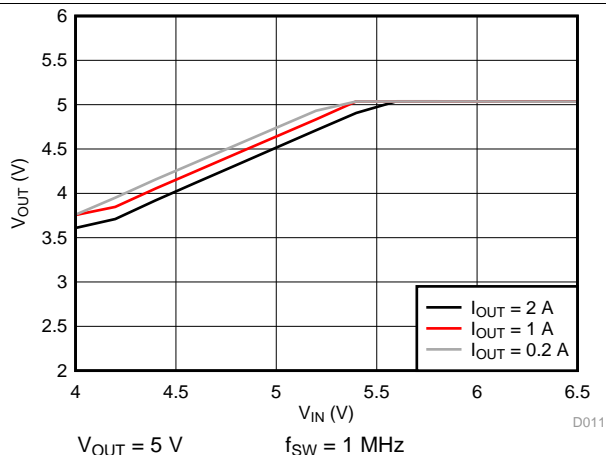


Figure 7. Dropout Curve

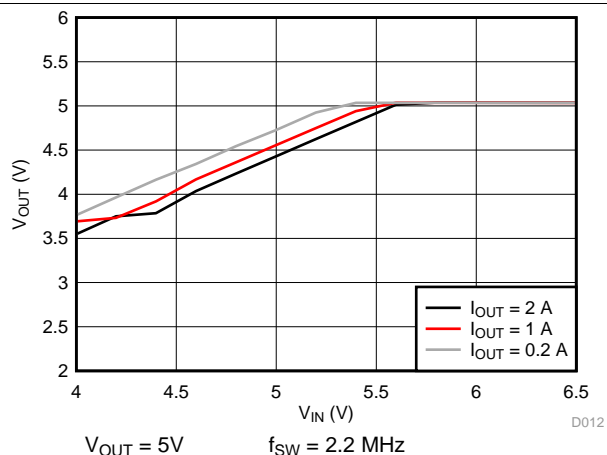


Figure 8. Dropout Curve

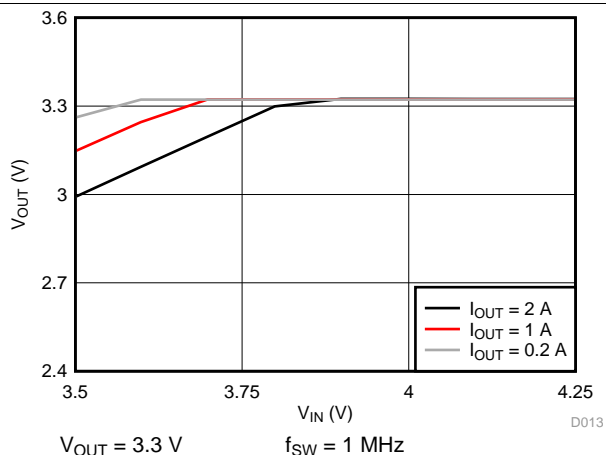


Figure 9. Dropout Curve

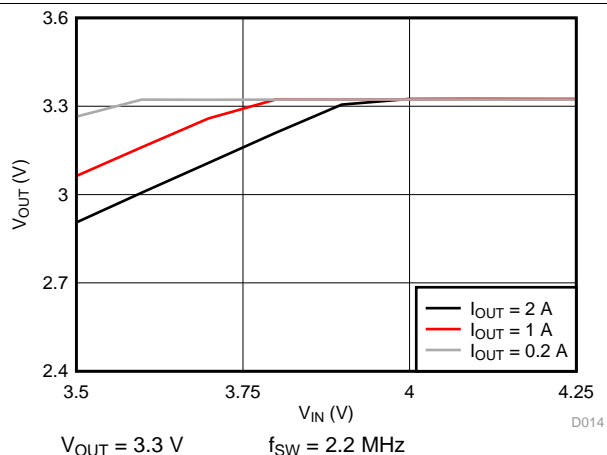


Figure 10. Dropout Curve

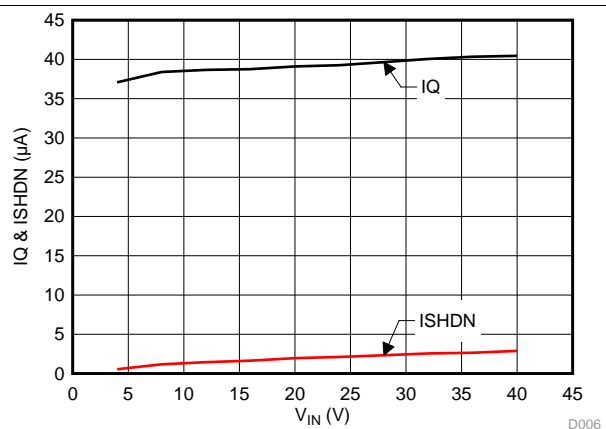


Figure 11. Shut-down Current and Quiescent Current

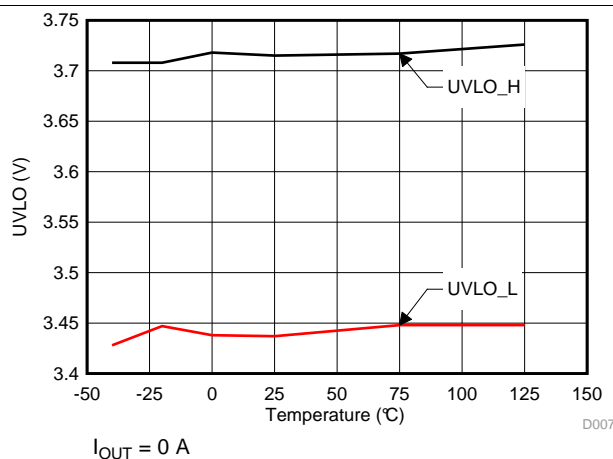


Figure 12. UVLO Threshold

8 Detailed Description

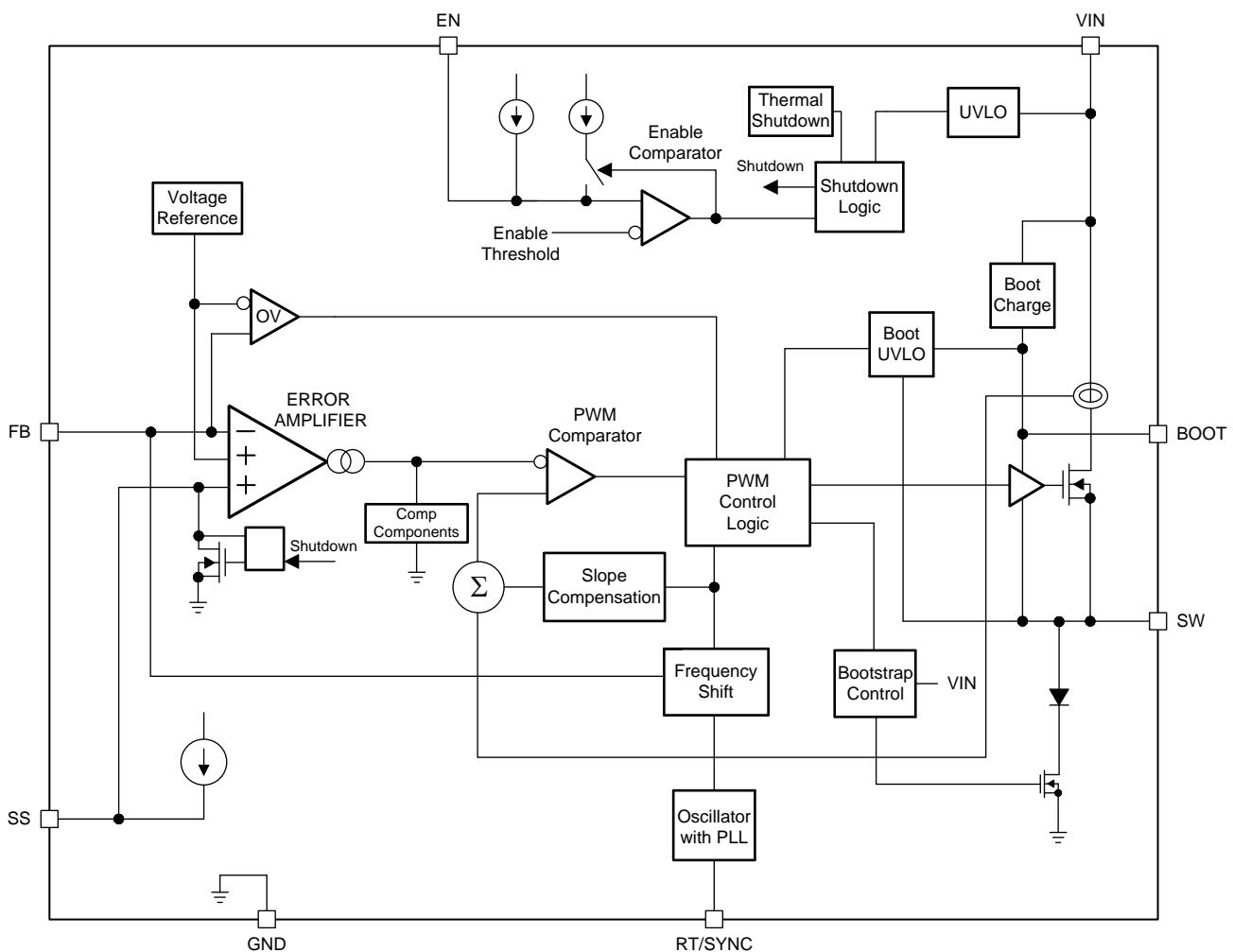
8.1 Overview

The LMR14020 SIMPLE SWITCHER® regulator is an easy to use step-down DC-DC converter that operates from 4.0 V to 40 V supply voltage. It integrates a 90 mΩ (typical) high-side MOSFET, and is capable of delivering up to 2 A DC load current with exceptional efficiency and thermal performance in a very small solution size. The operating current is typically 40 μA under no load condition (not switching). When the device is disabled, the supply current is typically 1 μA. An extended family is available in 3.5 A and 5 A load options in pin to pin compatible packages.

The LMR14020 implements constant frequency peak current mode control with Sleep-mode at light load to achieve high efficiency. The device is internally compensated, which reduces design time, and requires fewer external components. The switching frequency is programmable from 200 kHz to 2.5 MHz by an external resistor R_T . The LMR14020 is also capable of synchronization to an external clock within the 250 kHz to 2.3 MHz frequency range, which allows the device to be optimized to fit small board space at higher frequency, or high efficient power conversion at lower frequency.

Other optional features are included for more comprehensive system requirements, including precision enable, adjustable soft-start time, and approximate 97% duty cycle by BOOT capacitor recharge circuit. These features provide a flexible and easy to use platform for a wide range of applications. Protection features include over temperature shutdown, V_{OUT} over voltage protection (OVP), V_{IN} under-voltage lockout (UVLO), cycle-by-cycle current limit, and short-circuit protection with frequency fold-back.

8.2 Functional Block Diagram



8.3 Feature Description

8.3.1 Fixed Frequency Peak Current Mode Control

The following operation description of the LMR14020 will refer to the Function Block Diagram and to the waveforms in Figure 13. LMR14020 output voltage is regulated by turning on the high-side N-MOSFET with controlled ON time. During high-side switch ON time, the SW pin voltage swings up to approximately V_{IN} , and the inductor current i_L increase with linear slope $(V_{IN} - V_{OUT}) / L$. When high-side switch is off, inductor current discharges through freewheel diode with a slope of $-V_{OUT} / L$. The control parameter of Buck converter is defined as Duty Cycle $D = t_{ON} / T_{SW}$, where t_{ON} is the high-side switch ON time and T_{SW} is the switching period. The regulator control loop maintains a constant output voltage by adjusting the duty cycle D . In an ideal Buck converter, where losses are ignored, D is proportional to the output voltage and inversely proportional to the input voltage: $D = V_{OUT} / V_{IN}$.

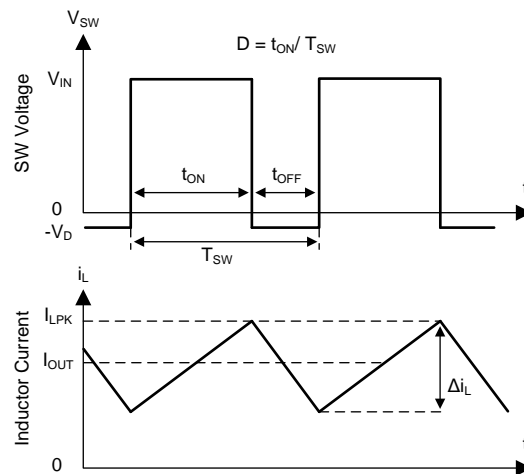


Figure 13. SW Node and Inductor Current Waveforms in Continuous Conduction Mode (CCM)

The LMR14020 employs fixed frequency peak current mode control. A voltage feedback loop is used to get accurate DC voltage regulation by adjusting the peak current command based on voltage offset. The peak inductor current is sensed from the high-side switch and compared to the peak current to control the ON time of the high-side switch. The voltage feedback loop is internally compensated, which allows for fewer external components, makes it easy to design, and provides stable operation with almost any combination of output capacitors. The regulator operates with fixed switching frequency at normal load condition. At very light load, the LMR14020 will operate in Sleep-mode to maintain high efficiency and the switching frequency will decrease with reduced load current.

8.3.2 Slope Compensation

The LMR14020 adds a compensating ramp to the MOSFET switch current sense signal. This slope compensation prevents sub-harmonic oscillations at duty cycle greater than 50%. The peak current limit of the high-side switch is not affected by the slope compensation and remains constant over the full duty cycle range.

8.3.3 Sleep-mode

The LMR14020 operates in Sleep-mode at light load currents to improve efficiency by reducing switching and gate drive losses. If the output voltage is within regulation and the peak switch current at the end of any switching cycle is below the current threshold of 300 mA, the device enters Sleep-mode. The Sleep-mode current threshold is the peak switch current level corresponding to a nominal internal COMP voltage of 400 mV.

When in Sleep-mode, the internal COMP voltage is clamped at 400 mV and the high-side MOSFET is inhibited, and the device draws only 40 μA (typical) input quiescent current. Since the device is not switching, the output voltage begins to decay. The voltage control loop responds to the falling output voltage by increasing the internal COMP voltage. The high-side MOSFET is enabled and switching resumes when the error amplifier lifts internal COMP voltage above 400 mV. The output voltage recovers to the regulated value, and internal COMP voltage eventually falls below the Sleep-mode threshold at which time the device again enters Sleep-mode.

Feature Description (continued)

8.3.4 Low Dropout Operation and Bootstrap Voltage (BOOT)

The LMR14020 provides an integrated bootstrap voltage regulator. A small capacitor between the BOOT and SW pins provides the gate drive voltage for the high-side MOSFET. The BOOT capacitor is refreshed when the high-side MOSFET is off and the external low side diode conducts. The recommended value of the BOOT capacitor is 0.1 μF . A ceramic capacitor with an X7R or X5R grade dielectric with a voltage rating of 16 V or higher is recommended for stable performance over temperature and voltage.

When operating with a low voltage difference from input to output, the high-side MOSFET of the LMR14020 will operate at approximate 97% duty cycle. When the high-side MOSFET is continuously on for 5 or 6 switching cycles (5 or 6 switching cycles for frequency lower than 1 MHz, and 10 or 11 switching cycles for frequency higher than 1MHz) and the voltage from BOOT to SW drops below 3.2 V, the high-side MOSFET is turned off and an integrated low side MOSFET pulls SW low to recharge the BOOT capacitor.

Since the gate drive current sourced from the BOOT capacitor is small, the high-side MOSFET can remain on for many switching cycles before the MOSFET is turned off to refresh the capacitor. Thus the effective duty cycle of the switching regulator can be high, approaching 97%. The effective duty cycle of the converter during dropout is mainly influenced by the voltage drops across the power MOSFET, the inductor resistance, the low side diode voltage and the printed circuit board resistance.

8.3.5 Adjustable Output Voltage

The internal voltage reference produces a precise 0.75 V (typical) voltage reference over the operating temperature. The output voltage is set by a resistor divider from output voltage to the FB pin. It is recommended to use 1% tolerance or better and temperature coefficient of 100 ppm or lower divider resistors. Select the low side resistor R_{FBB} for the desired divider current and use Equation 1 to calculate high-side R_{FBT} . Larger value divider resistors are good for efficiency at light load. However, if the values are too high, the regulator will be more susceptible to noise and voltage errors from the FB input current may become noticeable. R_{FBB} in the range from 10 k Ω to 100 k Ω is recommended for most applications.

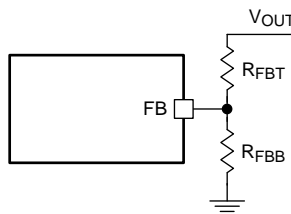


Figure 14. Output Voltage Setting

$$R_{\text{FBT}} = \frac{V_{\text{OUT}} - 0.75}{0.75} R_{\text{FBB}}$$

(1)

8.3.6 Enable and Adjustable Under-voltage Lockout

The LMR14020 is enabled when the VIN pin voltage rises above 3.7 V (typical) and the EN pin voltage exceeds the enable threshold of 1.2 V (typical). The LMR14020 is disabled when the VIN pin voltage falls below 3.52 V (typical) or when the EN pin voltage is below 1.2 V. The EN pin has an internal pull-up current source (typically $I_{\text{EN}} = 1 \mu\text{A}$) that enables operation of the LMR14020 when the EN pin is floating.

Many applications will benefit from the employment of an enable divider R_{ENT} and R_{ENB} in Figure 15 to establish a precision system UVLO level for the stage. System UVLO can be used for supplies operating from utility power as well as battery power. It can be used for sequencing, ensuring reliable operation, or supply protection, such as a battery. An external logic signal can also be used to drive EN input for system sequencing and protection.

When EN terminal voltage exceeds 1.2 V, an additional hysteresis current (typically $I_{\text{HYS}} = 3.6 \mu\text{A}$) is sourced out of EN terminal. When the EN terminal is pulled below 1.2 V, I_{HYS} current is removed. This additional current facilitates adjustable input voltage UVLO hysteresis. Use Equation 2 and Equation 3 to calculate R_{ENT} and R_{ENB} for desired UVLO hysteresis voltage.

Feature Description (continued)

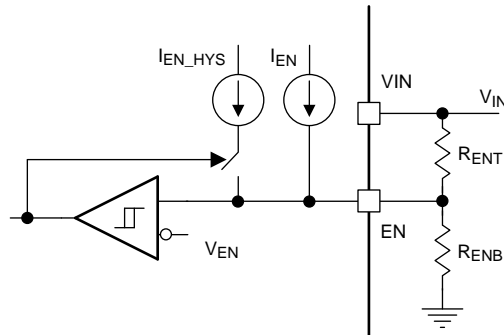


Figure 15. System UVLO By Enable Dividers

$$R_{ENT} = \frac{V_{START} - V_{STOP}}{I_{HYS}} \quad (2)$$

$$R_{ENB} = \frac{V_{EN}}{\frac{V_{START} - V_{EN}}{R_{ENT}} + I_{EN}} \quad (3)$$

where V_{START} is the desired voltage threshold to enable LMR14020, V_{STOP} is the desired voltage threshold to disable device.

8.3.7 External Soft-start

The LMR14020 has soft-start pin for programmable output ramp up time. The soft-start feature is used to prevent inrush current impacting the LMR14020 and its load when power is first applied. The soft-start time can be programmed by connecting an external capacitor C_{SS} from SS pin to GND. An internal current source (typically $I_{SS} = 3 \mu A$) charges C_{SS} and generates a ramp from 0 V to V_{REF} . The soft-start time can be calculated by Equation 4:

$$t_{SS}(ms) = \frac{C_{SS}(nF) \times V_{REF}(V)}{I_{SS}(\mu A)} \quad (4)$$

The internal soft-start resets while device is disabled or in thermal shutdown.

8.3.8 Switching Frequency and Synchronization (RT/SYNC)

The switching frequency of the LMR14020 can be programmed by the resistor R_T from the RT/SYNC pin and GND pin. The RT/SYNC pin can't be left floating or shorted to ground. To determine the timing resistance for a given switching frequency, use Equation 5 or the curve in Figure 16. Table 1 gives typical R_T values for a given f_{SW} .

$$R_T(k\Omega) = 32537 \times f_{SW}(kHz)^{-1.045} \quad (5)$$

Feature Description (continued)

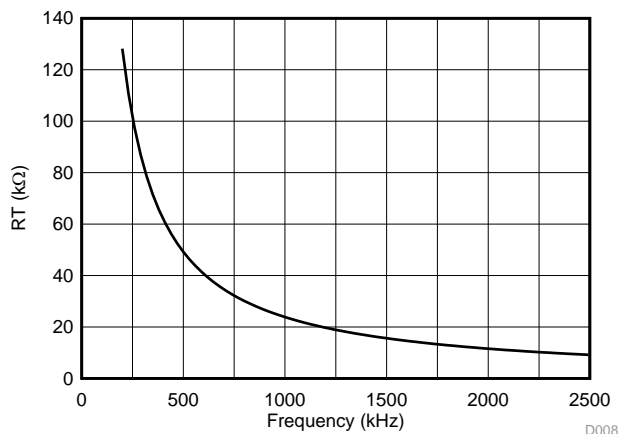


Figure 16. RT vs Frequency Curve

Table 1. Typical Frequency Setting RT Resistance

f_{sw} (kHz)	R_T (kΩ)
200	127
350	71.5
500	49.9
750	32.4
1000	23.7
1500	15.8
2000	11.5
2200	10.5

The LMR14020 switching action can also be synchronized to an external clock from 250 kHz to 2.3 MHz. Connect a square wave to the RT/SYNC pin through either circuit network shown in Figure 17. Internal oscillator is synchronized by the falling edge of external clock. The recommendations for the external clock include: high level no lower than 1.7 V, low level no higher than 0.5 V and have a pulse width greater than 30 ns. When using a low impedance signal source, the frequency setting resistor R_T is connected in parallel with an AC coupling capacitor C_{COUP} to a termination resistor R_{TERM} (e.g., 50 Ω). The two resistors in series provide the default frequency setting resistance when the signal source is turned off. A 10 pF ceramic capacitor can be used for C_{COUP} . Figure 18, Figure 19 and Figure 20 show the device synchronized to an external system clock.

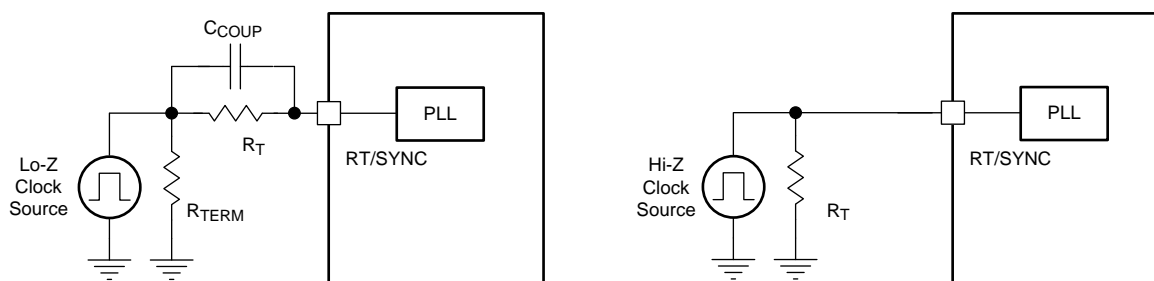


Figure 17. Synchronizing to an External Clock

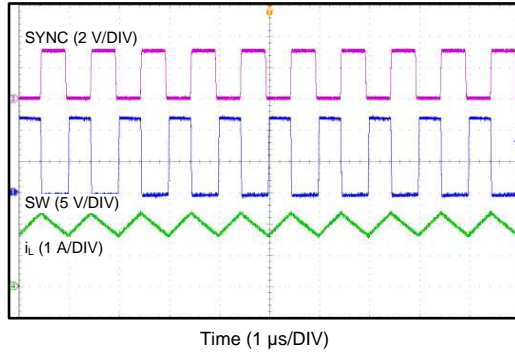


Figure 18. Synchronizing in CCM

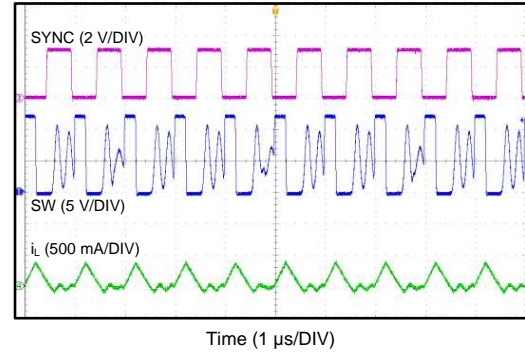


Figure 19. Synchronizing in DCM

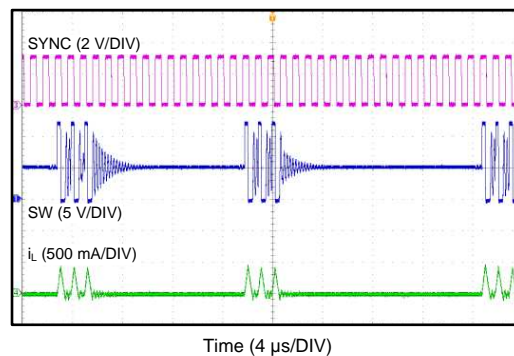


Figure 20. Synchronizing in Sleep-mode Mode

Equation 6 calculates the maximum switching frequency limitation set by the minimum controllable on time and the input to output step down ratio. Setting the switching frequency above this value will cause the regulator to skip switching pulses to achieve the low duty cycle required at maximum input voltage.

$$f_{SW(max)} = \frac{1}{t_{ON}} \times \left(\frac{I_{OUT} \times R_{IND} + V_{OUT} + V_D}{V_{IN_MAX} - I_{OUT} \times R_{DS_ON} + V_D} \right) \quad (6)$$

where

- I_{OUT} = Output current
- R_{IND} = Inductor series resistance
- V_{IN_MAX} = Maximum input voltage
- V_{OUT} = Output voltage
- V_D = Diode voltage drop
- R_{DS_ON} = High-side MOSFET switch on resistance
- t_{ON} = Minimum on time

8.3.9 Over Current and Short Circuit Protection

The LMR14020 is protected from over current condition by cycle-by-cycle current limiting on the peak current of the high-side MOSFET. High-side MOSFET over-current protection is implemented by the nature of the Peak Current Mode control. The high-side switch current is compared to the output of the Error Amplifier (EA) minus slope compensation every switching cycle. Please refer to Functional Block Diagram for more details. The peak current of high-side switch is limited by a clamped maximum peak current threshold which is constant. So the peak current limit of the high-side switch is not affected by the slope compensation and remains constant over the full duty cycle range.

LMR14020

ZHCSDJ2A – FEBRUARY 2015 – REVISED APRIL 2015

www.ti.com.cn

The LMR14020 also implements a frequency fold-back to protect the converter in severe over-current or short conditions. The oscillator frequency is divided by 2, 4, and 8 as the FB pin voltage decrease to 75%, 50%, 25% of V_{REF} . The frequency fold-back increases the off time by increasing the period of the switching cycle, so that it provides more time for the inductor current to ramp down and leads to a lower average inductor current. Lower frequency also means lower switching loss. Frequency fold-back reduces power dissipation and prevents overheating and potential damage to the device.

8.3.10 Overvoltage Protection

The LMR14020 employs an output overvoltage protection (OVP) circuit to minimize voltage overshoot when recovering from output fault conditions or strong unload transients in designs with low output capacitance. The OVP feature minimizes output overshoot by turning off high-side switch immediately when FB voltage reaches to the rising OVP threshold which is nominally 109% of the internal voltage reference V_{REF} . When the FB voltage drops below the falling OVP threshold which is nominally 107% of V_{REF} , the high-side MOSFET resumes normal operation.

8.3.11 Thermal Shutdown

The LMR14020 provides an internal thermal shutdown to protect the device when the junction temperature exceeds 170°C (typical). The high-side MOSFET stops switching when thermal shutdown activates. Once the die temperature falls below 158°C (typical), the device reinitiates the power up sequence controlled by the internal soft-start circuitry.

9 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

9.1 Application Information

The LMR14020 is a step down DC-to-DC regulator. It is typically used to convert a higher DC voltage to a lower DC voltage with a maximum output current of 2 A. The following design procedure can be used to select components for the LMR14020. This section presents a simplified discussion of the design process.

9.2 Typical Application

The LMR14020 only requires a few external components to convert from wide voltage range supply to a fixed output voltage. A schematic of 5 V/2 A application circuit is shown in [Figure 21](#). The external components have to fulfill the needs of the application, but also the stability criteria of the device's control loop.

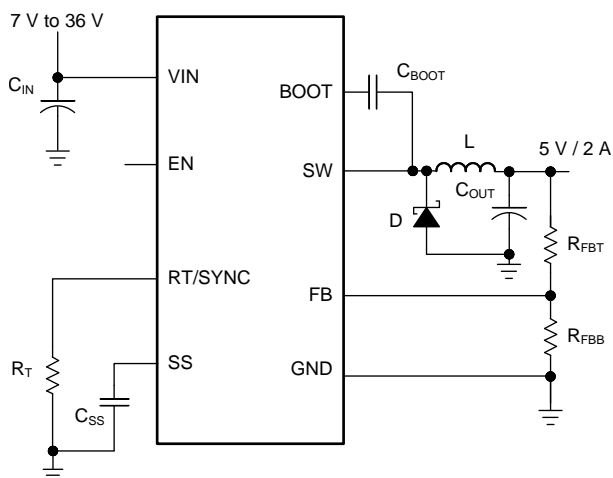


Figure 21. Application Circuit, 5V Output

9.2.1 Design Requirements

This example details the design of a high frequency switching regulator using ceramic output capacitors. A few parameters must be known in order to start the design process. These parameters are typically determined at the system level:

Input Voltage, V_{IN}	7 V to 36 V, Typical 12 V
Output Voltage, V_{OUT}	5.0 V
Maximum Output Current I_{O_MAX}	2 A
Transient Response 0.2 A to 2 A	5%
Output Voltage Ripple	50 mV
Input Voltage Ripple	400 mV
Switching Frequency f_{SW}	1 MHz
Soft-start time	5 ms

9.2.2 Detailed Design Procedure

9.2.2.1 Output Voltage Set-Point

The output voltage of LMR14020 is externally adjustable using a resistor divider network. The divider network is comprised of top feedback resistor R_{FBT} and bottom feedback resistor R_{FBB} . Equation 7 is used to determine the output voltage:

$$R_{FBT} = \frac{V_{OUT} - 0.75}{0.75} R_{FBB} \quad (7)$$

Choose the value of R_{FBT} to be 100 k Ω . With the desired output voltage set to 5 V and the $V_{FB} = 0.75$ V, the R_{FBB} value can then be calculated using Equation 7. The formula yields to a value 17.65 k Ω . Choose the closest available value of 17.8 k Ω for R_{FBB} .

9.2.2.2 Switching Frequency

For desired frequency, use Equation 8 to calculate the required value for R_T .

$$R_T(k\Omega) = 32537 \times f_{SW}(kHz)^{-1.045} \quad (8)$$

For 1 MHz, the calculated R_T is 23.8 k Ω and standard value 23.7 k Ω can be used to set the switching frequency at 1 MHz.

9.2.2.3 Output Inductor Selection

The most critical parameters for the inductor are the inductance, saturation current and the RMS current. The inductance is based on the desired peak-to-peak ripple current Δi_L . Since the ripple current increases with the input voltage, the maximum input voltage is always used to calculate the minimum inductance L_{MIN} . Use Equation 9 to calculate the minimum value of the output inductor. K_{IND} is a coefficient that represents the amount of inductor ripple current relative to the maximum output current. A reasonable value of K_{IND} should be 20%-40%. During an instantaneous short or over current operation event, the RMS and peak inductor current can be high. The inductor current rating should be higher than current limit.

$$\Delta i_L = \frac{V_{OUT} \times (V_{IN_MAX} - V_{OUT})}{V_{IN_MAX} \times L \times f_{SW}} \quad (9)$$

$$L_{MIN} = \frac{V_{IN_MAX} - V_{OUT}}{I_{OUT} \times K_{IND}} \times \frac{V_{OUT}}{V_{IN_MAX} \times f_{SW}} \quad (10)$$

In general, it is preferable to choose lower inductance in switching power supplies, because it usually corresponds to faster transient response, smaller DCR, and reduced size for more compact designs. But too low of an inductance can generate too large of an inductor current ripple such that over current protection at the full load could be falsely triggered. It also generates more conduction loss since the RMS current is slightly higher. Larger inductor current ripple also implies larger output voltage ripple with same output capacitors. With peak current mode control, it is not recommended to have too small of an inductor current ripple. A larger peak current ripple improves the comparator signal to noise ratio.

For this design example, choose $K_{IND} = 0.4$, the minimum inductor value is calculated to be 5.38 μ H, and a nearest standard value is chosen: 5.5 μ H. A standard 5.5 μ H ferrite inductor with a capability of 3 A RMS current and 4 A saturation current can be used.

9.2.2.4 Output Capacitor Selection

The output capacitor(s), C_{OUT} , should be chosen with care since it directly affects the steady state output voltage ripple, loop stability and the voltage over/undershoot during load current transients.

The output ripple is essentially composed of two parts. One is caused by the inductor current ripple going through the Equivalent Series Resistance (ESR) of the output capacitors:

$$\Delta V_{OUT_ESR} = \Delta i_L \times ESR = K_{IND} \times I_{OUT} \times ESR \quad (11)$$

The other is caused by the inductor current ripple charging and discharging the output capacitors:

$$\Delta V_{OUT_C} = \frac{\Delta i_L}{8 \times f_{SW} \times C_{OUT}} = \frac{K_{IND} \times I_{OUT}}{8 \times f_{SW} \times C_{OUT}} \quad (12)$$

The two components in the voltage ripple are not in phase, so the actual peak-to-peak ripple is smaller than the sum of two peaks.

Output capacitance is usually limited by transient performance specifications if the system requires tight voltage regulation with presence of large current steps and fast slew rate. When a fast large load increase happens, output capacitors provide the required charge before the inductor current can slew up to the appropriate level. The regulator's control loop usually needs three or more clock cycles to respond to the output voltage droop. The output capacitance must be large enough to supply the current difference for three clock cycles to maintain the output voltage within the specified range. Equation 13 shows the minimum output capacitance needed for specified output undershoot. When a sudden large load decrease happens, the output capacitors absorb energy stored in the inductor. The catch diode can't sink current so the energy stored in the inductor results in an output voltage overshoot. Equation 14 calculates the minimum capacitance required to keep the voltage overshoot within a specified range.

$$C_{OUT} > \frac{3 \times (I_{OH} - I_{OL})}{f_{SW} \times V_{US}} \quad (13)$$

$$C_{OUT} > \frac{I_{OH}^2 - I_{OL}^2}{(V_{OUT} + V_{OS})^2 - V_{OUT}^2} \times L \quad (14)$$

where

- K_{IND} = Ripple ratio of the inductor ripple current ($\Delta I_L / I_{OUT}$)
- I_{OL} = Low level output current during load transient
- I_{OH} = High level output current during load transient
- V_{US} = Target output voltage undershoot
- V_{OS} = Target output voltage overshoot

For this design example, the target output ripple is 50 mV. Presuppose $\Delta V_{OUT_ESR} = \Delta V_{OUT_C} = 50$ mV, and chose $K_{IND} = 0.4$. Equation 11 yields ESR no larger than 62.5 mΩ and Equation 12 yields C_{OUT} no smaller than 2 μF. For the target over/undershoot range of this design, $V_{US} = V_{OS} = 5\% \times V_{OUT} = 250$ mV. The C_{OUT} can be calculated to be no smaller than 21.6 μF and 4.1 μF by Equation 13 and Equation 14 respectively. For stability consideration, one 47 μF output capacitor is needed at least. In summary, the most stringent criteria for the output capacitor is 47 μF. One 47 μF, 16 V, X7R ceramic capacitors with 5 mΩ ESR is used.

9.2.2.5 Schottky Diode Selection

The breakdown voltage rating of the diode is preferred to be 25% higher than the maximum input voltage. The current rating for the diode should be equal to the maximum output current for best reliability in most applications. In cases where the input voltage is much greater than the output voltage the average diode current is lower. In this case it is possible to use a diode with a lower average current rating, approximately $(1-D) \times I_{OUT}$ however the peak current rating should be higher than the maximum load current. A 2.5 A to 3 A rated diode is a good starting point.

9.2.2.6 Input Capacitor Selection

The LMR14020 device requires high frequency input decoupling capacitor(s) and a bulk input capacitor, depending on the application. The typical recommended value for the high frequency decoupling capacitor is 4.7 μF to 10 μF. A high-quality ceramic capacitor type X5R or X7R with sufficiency voltage rating is recommended. To compensate the derating of ceramic capacitors, a voltage rating of twice the maximum input voltage is recommended. Additionally, some bulk capacitance can be required, especially if the LMR14020 circuit is not located within approximately 5 cm from the input voltage source. This capacitor is used to provide damping to the voltage spike due to the lead inductance of the cable or the trace. For this design, two 2.2 μF, X7R ceramic capacitors rated for 100 V are used. A 0.1 μF for high-frequency filtering and place it as close as possible to the device pins.

9.2.2.7 Bootstrap Capacitor Selection

Every LMR14020 design requires a bootstrap capacitor (C_{BOOT}). The recommended capacitor is 0.1 μF and rated 16 V or higher. The bootstrap capacitor is located between the SW pin and the BOOT pin. The bootstrap capacitor must be a high-quality ceramic type with an X7R or X5R grade dielectric for temperature stability.

9.2.2.8 Soft-start Capacitor Selection

Use [Equation 15](#) in order to calculate the soft-start capacitor value:

$$C_{SS}(\text{nF}) = \frac{t_{SS}(\text{ms}) \times I_{SS}(\mu\text{A})}{V_{REF}(\text{V})} \quad (15)$$

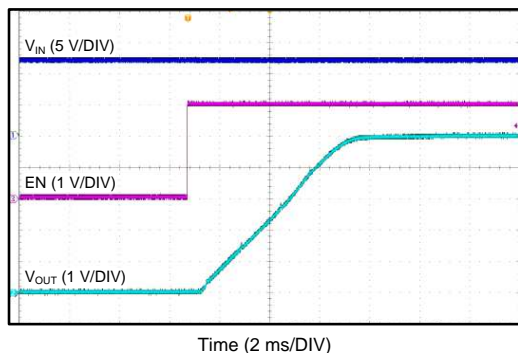
where

- C_{SS} = Soft-start capacitor value
- I_{SS} = Soft-start charging current (3 μA)
- t_{SS} = Desired soft-start time

For the desired soft-start time of 5 ms and soft-start charging current of 3.0 μA , the [Equation 15](#) yields a soft-start capacitor value of 20 nF, a standard 22 nF ceramic capacitor is used.

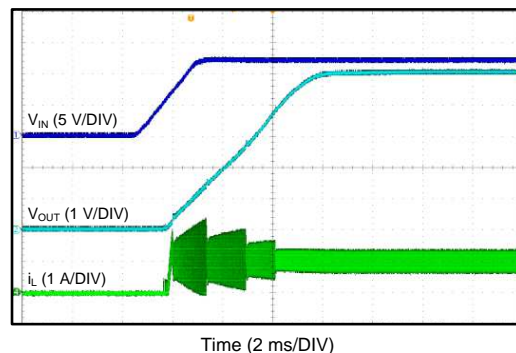
9.2.3 Application Curves

Unless otherwise specified the following conditions apply: $V_{IN} = 12\text{ V}$, $f_{SW} = 1\text{ MHz}$, $L = 5.5\text{ }\mu\text{H}$, $C_{OUT} = 47\text{ }\mu\text{F}$, $T_A = 25^\circ\text{C}$.



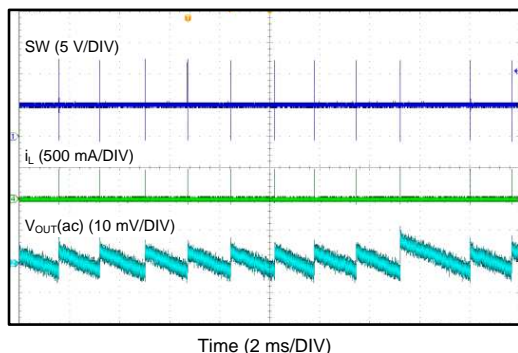
$V_{IN} = 12\text{ V}$ $V_{OUT} = 5\text{ V}$ $I_{OUT} = 1\text{ A}$

Figure 22. Start-up By EN



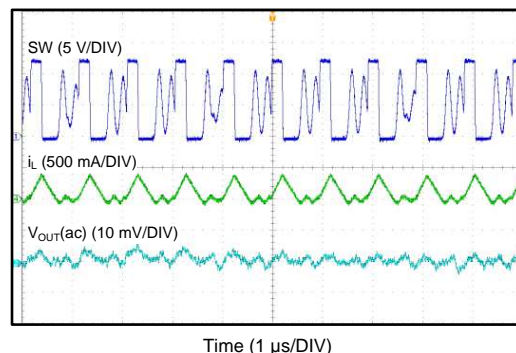
$V_{IN} = 12\text{ V}$ $V_{OUT} = 5\text{ V}$ $I_{OUT} = 1\text{ A}$

Figure 23. Start-up By V_{IN}



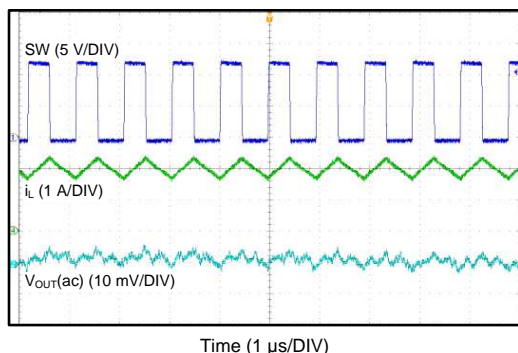
$V_{IN} = 12\text{ V}$ $V_{OUT} = 5\text{ V}$ $I_{OUT} = 0\text{ A}$

Figure 24. Sleep-mode



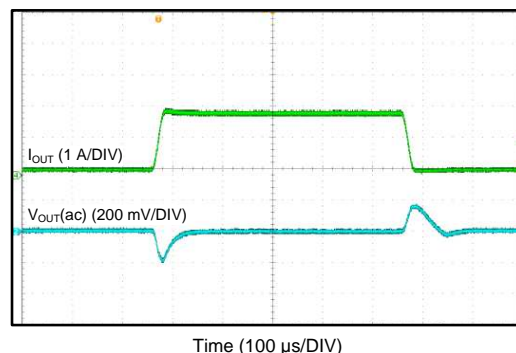
$V_{IN} = 12\text{ V}$ $V_{OUT} = 5\text{ V}$ $I_{OUT} = 100\text{ mA}$

Figure 25. DCM Mode



$V_{IN} = 12\text{ V}$ $V_{OUT} = 5\text{ V}$ $I_{OUT} = 2\text{ A}$

Figure 26. CCM Mode



I_{OUT} : 10% → 100%
of 2 A Slew rate = 100
mA/μs

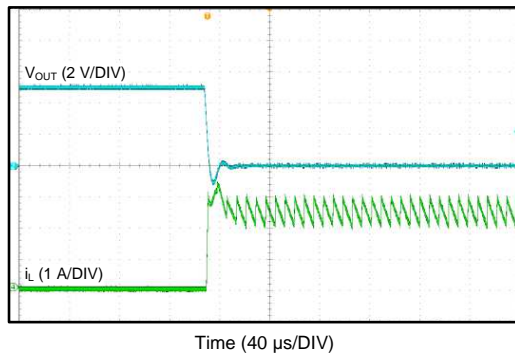
Figure 27. Load Transient

LMR14020

ZHCSDJ2A – FEBRUARY 2015 – REVISED APRIL 2015

www.ti.com.cn

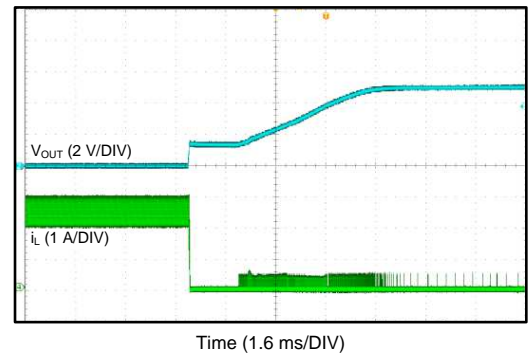
Unless otherwise specified the following conditions apply: $V_{IN} = 12\text{ V}$, $f_{SW} = 1\text{ MHz}$, $L = 5.5\text{ }\mu\text{H}$, $C_{OUT} = 47\text{ }\mu\text{F}$, $T_A = 25^\circ\text{C}$.



$V_{IN} = 12\text{ V}$

$V_{OUT} = 5\text{ V}$

Figure 28. Output Short



$V_{IN} = 12\text{ V}$

$V_{OUT} = 5\text{ V}$

Figure 29. Output Short Recovery

10 Power Supply Recommendations

The LMR14020 is designed to operate from an input voltage supply range between 4 V and 40 V. This input supply should be able to withstand the maximum input current and maintain a stable voltage. The resistance of the input supply rail should be low enough that an input current transient does not cause a high enough drop at the LMR14020 supply voltage that can cause a false UVLO fault triggering and system reset. If the input supply is located more than a few inches from the LMR14020, additional bulk capacitance may be required in addition to the ceramic input capacitors. The amount of bulk capacitance is not critical, but a 47 μ F or 100 μ F electrolytic capacitor is a typical choice .

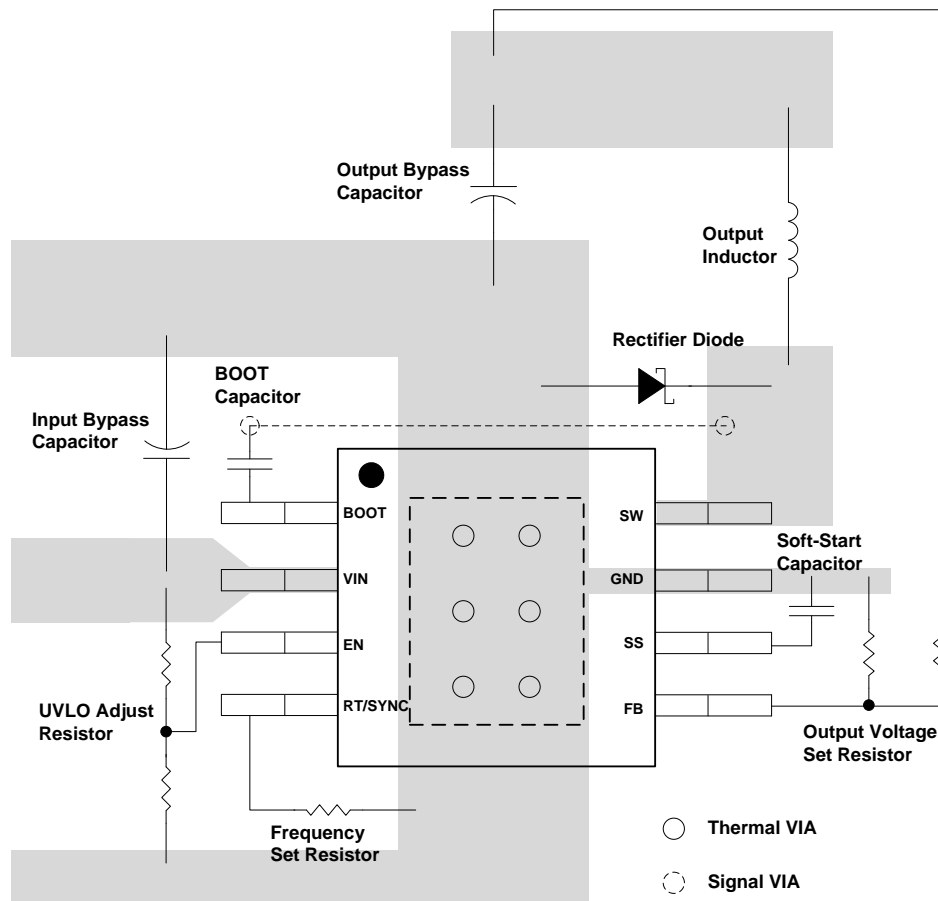
11 Layout

11.1 Layout Guidelines

Layout is a critical portion of good power supply design. The following guidelines will help users design a PCB with the best power conversion performance, thermal performance, and minimized generation of unwanted EMI.

1. The feedback network, resistor R_{FBT} and R_{FBB} , should be kept close to the FB pin. V_{OUT} sense path away from noisy nodes and preferably through a layer on the other side of a shielding layer .
2. The input bypass capacitor C_{IN} must be placed as close as possible to the VIN pin and ground. Grounding for both the input and output capacitors should consist of localized top side planes that connect to the GND pin and PAD .
3. The inductor L should be placed close to the SW pin to reduce magnetic and electrostatic noise.
4. The output capacitor, C_{OUT} should be placed close to the junction of L and the diode D. The L, D, and C_{OUT} trace should be as short as possible to reduce conducted and radiated noise and increase overall efficiency.
5. The ground connection for the diode, C_{IN} , and C_{OUT} should be as small as possible and tied to the system ground plane in only one spot (preferably at the C_{OUT} ground point) to minimize conducted noise in the system ground plane
6. For more detail on switching power supply layout considerations see Application Note AN-1149

11.2 Layout Example



12 器件和文档支持

12.1 商标

PowerPAD is a trademark of Texas Instruments.

SIMPLE SWITCHER is a registered trademark of Texas Instruments.

All other trademarks are the property of their respective owners.

12.2 静电放电警告



这些装置包含有限的内置 ESD 保护。存储或装卸时，应将导线一起截短或将装置放置于导电泡棉中，以防止 MOS 门极遭受静电损伤。

12.3 术语表

[SLYZ022](#) — *TI* 术语表。

这份术语表列出并解释术语、首字母缩略词和定义。

13 机械封装和可订购信息

以下页中包括机械封装和可订购信息。 这些信息是针对指定器件可提供的最新数据。 这些数据会在无通知且不对本文档进行修订的情况下发生改变。 欲获得该数据表的浏览器版本，请查阅左侧的导航栏。

重要声明

德州仪器(TI) 及其下属子公司有权根据 JESD46 最新标准, 对所提供的产品和服务进行更正、修改、增强、改进或其它更改, 并有权根据 JESD48 最新标准中止提供任何产品和服务。客户在下订单前应获取最新的相关信息, 并验证这些信息是否完整且是最新的。所有产品的销售都遵循在订单确认时所提供的TI 销售条款与条件。

TI 保证其所销售的组件的性能符合产品销售时 TI 半导体产品销售条件与条款的适用规范。仅在 TI 保证的范围内, 且 TI 认为 有必要时才会使用测试或其它质量控制技术。除非适用法律做出了硬性规定, 否则没有必要对每种组件的所有参数进行测试。

TI 对应用帮助或客户产品设计不承担任何义务。客户应对其使用 TI 组件的产品和应用自行负责。为尽量减小与客户产品和应用相关的风险, 客户应提供充分的设计与操作安全措施。

TI 不对任何 TI 专利权、版权、屏蔽作品权或其它与使用了 TI 组件或服务的组合设备、机器或流程相关的 TI 知识产权中授予 的直接或隐含权限作出任何保证或解释。TI 所发布的与第三方产品或服务有关的信息, 不能构成从 TI 获得使用这些产品或服务 的许可、授权、或认可。使用此类信息可能需要获得第三方的专利权或其它知识产权方面的许可, 或是 TI 的专利权或其它 知识产权方面的许可。

对于 TI 的产品手册或数据表中 TI 信息的重要部分, 仅在没有对内容进行任何篡改且带有相关授权、条件、限制和声明的情况 下才允许进行复制。TI 对此类篡改过的文件不承担任何责任或义务。复制第三方的信息可能需要服从额外的限制条件。

在转售 TI 组件或服务时, 如果对该组件或服务参数的陈述与 TI 标明的参数相比存在差异或虚假成分, 则会失去相关 TI 组件 或服务的所有明示或暗示授权, 且这是不正当的、欺诈性商业行为。TI 对任何此类虚假陈述均不承担任何责任或义务。

客户认可并同意, 尽管任何应用相关信息或支持仍可能由 TI 提供, 但他们将独力负责满足与其产品及其应用中使用的 TI 产品 相关的所有法律、法规和安全相关要求。客户声明并同意, 他们具备制定与实施安全措施所需的全部专业技术和知识, 可预见 故障的危险后果、监测故障及其后果、降低有可能造成人身伤害的故障的发生机率并采取适当的补救措施。客户将全额赔偿因 在此类安全关键应用中使用任何 TI 组件而对 TI 及其代理造成的任何损失。

在某些场合中, 为了推进安全相关应用有可能对 TI 组件进行特别的促销。TI 的目标是利用此类组件帮助客户设计和创立其特 有的可满足适用的功能安全性标准和要求的终端产品解决方案。尽管如此, 此类组件仍然服从这些条款。

TI 组件未获得用于 FDA Class III (或类似的生命攸关医疗设备) 的授权许可, 除非各方授权官员已经达成了专门管控此类使 用的特别协议。

只有那些 TI 特别注明属于军用等级或“增强型塑料”的 TI 组件才是设计或专门用于军事/航空应用或环境的。购买者认可并同 意, 对并非指定面向军事或航空航天用途的 TI 组件进行军事或航空航天方面的应用, 其风险由客户单独承担, 并且由客户独 力负责满足与此类使用相关的所有法律和法规要求。

TI 已明确指定符合 ISO/TS16949 要求的产品, 这些产品主要用于汽车。在任何情况下, 因使用非指定产品而无法达到 ISO/TS16949 要求, TI 不承担任何责任。

	产品		应用
数字音频	www.ti.com.cn/audio	通信与电信	www.ti.com.cn/telecom
放大器和线性器件	www.ti.com.cn/amplifiers	计算机及周边	www.ti.com.cn/computer
数据转换器	www.ti.com.cn/dataconverters	消费电子	www.ti.com.cn/consumer-apps
DLP® 产品	www.dlp.com	能源	www.ti.com.cn/energy
DSP - 数字信号处理器	www.ti.com.cn/dsp	工业应用	www.ti.com.cn/industrial
时钟和计时器	www.ti.com.cn/clockandtimers	医疗电子	www.ti.com.cn/medical
接口	www.ti.com.cn/interface	安防应用	www.ti.com.cn/security
逻辑	www.ti.com.cn/logic	汽车电子	www.ti.com.cn/automotive
电源管理	www.ti.com.cn/power	视频和影像	www.ti.com.cn/video
微控制器 (MCU)	www.ti.com.cn/microcontrollers		
RFID 系统	www.ti.com.cn/rfidsys		
OMAP应用处理器	www.ti.com.cn/omap		
无线连通性	www.ti.com.cn/wirelessconnectivity	德州仪器在线技术支持社区	www.deyisupport.com

邮寄地址: 上海市浦东新区世纪大道1568号, 中建大厦32楼邮政编码: 200122
Copyright © 2015, 德州仪器半导体技术(上海)有限公司

PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead finish/ Ball material (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
LMR14020SDDA	ACTIVE	SO PowerPAD	DDA	8	75	RoHS & Green	NIPDAUAG	Level-2-260C-1 YEAR	-40 to 125	DB2SP	Samples
LMR14020SDDAR	ACTIVE	SO PowerPAD	DDA	8	2500	RoHS & Green	NIPDAUAG	Level-2-260C-1 YEAR	-40 to 125	DB2SP	Samples

(1) The marketing status values are defined as follows:

ACTIVE: Product device recommended for new designs.

LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

PREVIEW: Device has been announced but is not in production. Samples may or may not be available.

OBsolete: TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".

RoHS Exempt: TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

Green: TI defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JS709B low halogen requirements of <=1000ppm threshold. Antimony trioxide based flame retardants must also meet the <=1000ppm threshold requirement.

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

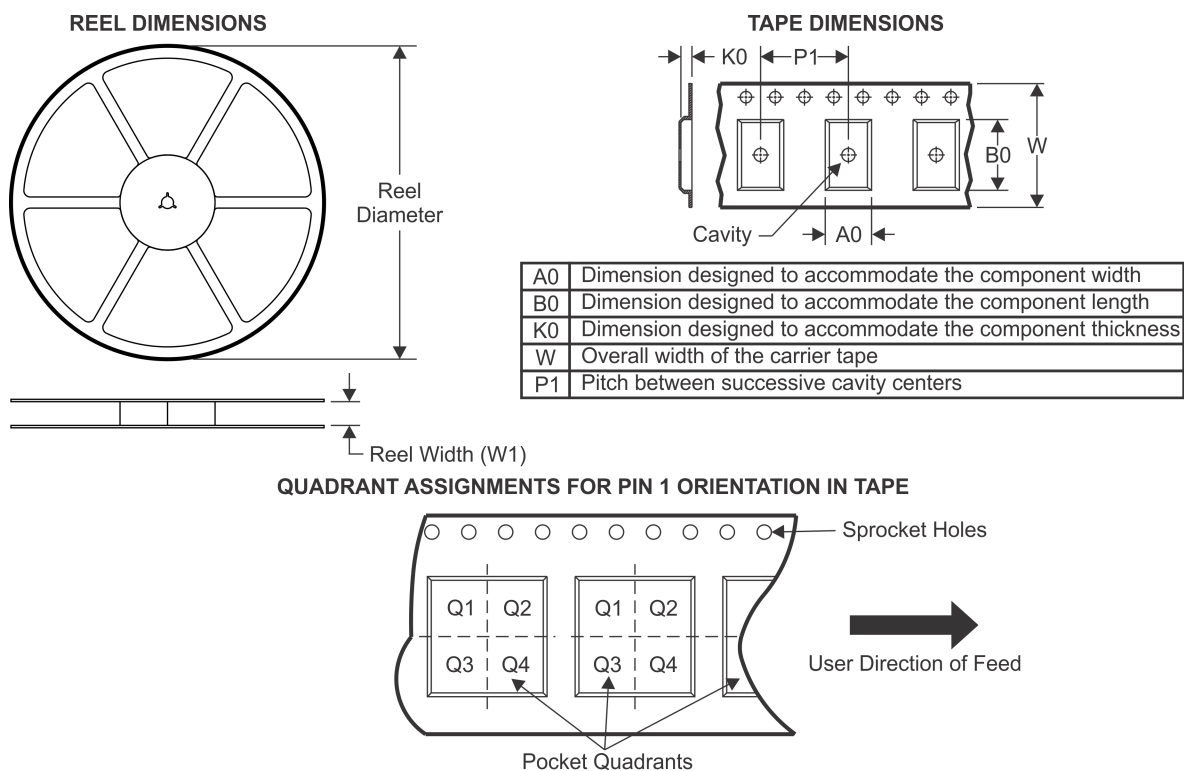
(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead finish/Ball material - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

Important Information and Disclaimer: The information provided on this page represents TI's knowledge and belief as of the date that it is provided. TI bases its knowledge and belief on information provided by third parties, and makes no representation or warranty as to the accuracy of such information. Efforts are underway to better integrate information from third parties. TI has taken and continues to take reasonable steps to provide representative and accurate information but may not have conducted destructive testing or chemical analysis on incoming materials and chemicals. TI and TI suppliers consider certain information to be proprietary, and thus CAS numbers and other limited information may not be available for release.

In no event shall TI's liability arising out of such information exceed the total purchase price of the TI part(s) at issue in this document sold by TI to Customer on an annual basis.

TAPE AND REEL INFORMATION


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LMR14020SDDAR	SO Power PAD	DDA	8	2500	330.0	12.8	6.4	5.2	2.1	8.0	12.0	Q1

TAPE AND REEL BOX DIMENSIONS

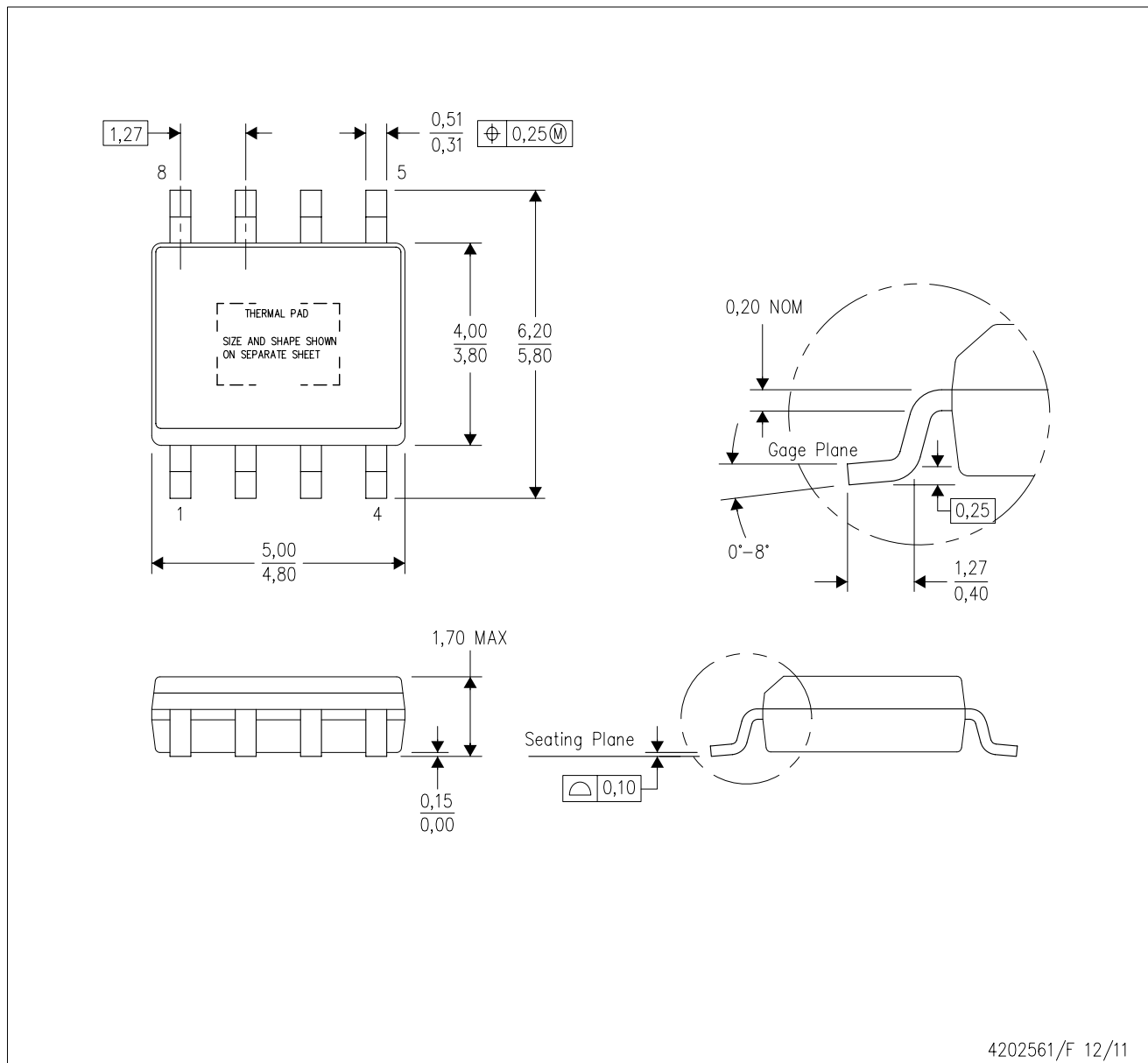


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LMR14020SDDAR	SO PowerPAD	DDA	8	2500	366.0	364.0	50.0

DDA (R-PDSO-G8)

PowerPAD™ PLASTIC SMALL-OUTLINE



- NOTES:
- All linear dimensions are in millimeters. Dimensioning and tolerancing per ASME Y14.5-1994.
 - This drawing is subject to change without notice.
 - Body dimensions do not include mold flash or protrusion not to exceed 0,15.
 - This package is designed to be soldered to a thermal pad on the board. Refer to Technical Brief, PowerPad Thermally Enhanced Package, Texas Instruments Literature No. SLMA002 for information regarding recommended board layout. This document is available at www.ti.com <<http://www.ti.com>>.
 - See the additional figure in the Product Data Sheet for details regarding the exposed thermal pad features and dimensions.
 - This package complies to JEDEC MS-012 variation BA

PowerPAD is a trademark of Texas Instruments.

DDA (R-PDSO-G8)

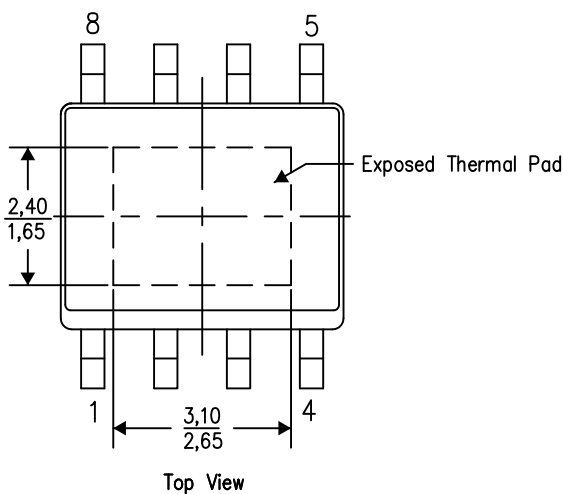
PowerPAD™ PLASTIC SMALL OUTLINE

THERMAL INFORMATION

This PowerPAD™ package incorporates an exposed thermal pad that is designed to be attached to a printed circuit board (PCB). The thermal pad must be soldered directly to the PCB. After soldering, the PCB can be used as a heatsink. In addition, through the use of thermal vias, the thermal pad can be attached directly to the appropriate copper plane shown in the electrical schematic for the device, or alternatively, can be attached to a special heatsink structure designed into the PCB. This design optimizes the heat transfer from the integrated circuit (IC).

For additional information on the PowerPAD package and how to take advantage of its heat dissipating abilities, refer to Technical Brief, PowerPAD Thermally Enhanced Package, Texas Instruments Literature No. SLMA002 and Application Brief, PowerPAD Made Easy, Texas Instruments Literature No. SLMA004. Both documents are available at www.ti.com.

The exposed thermal pad dimensions for this package are shown in the following illustration.



Exposed Thermal Pad Dimensions

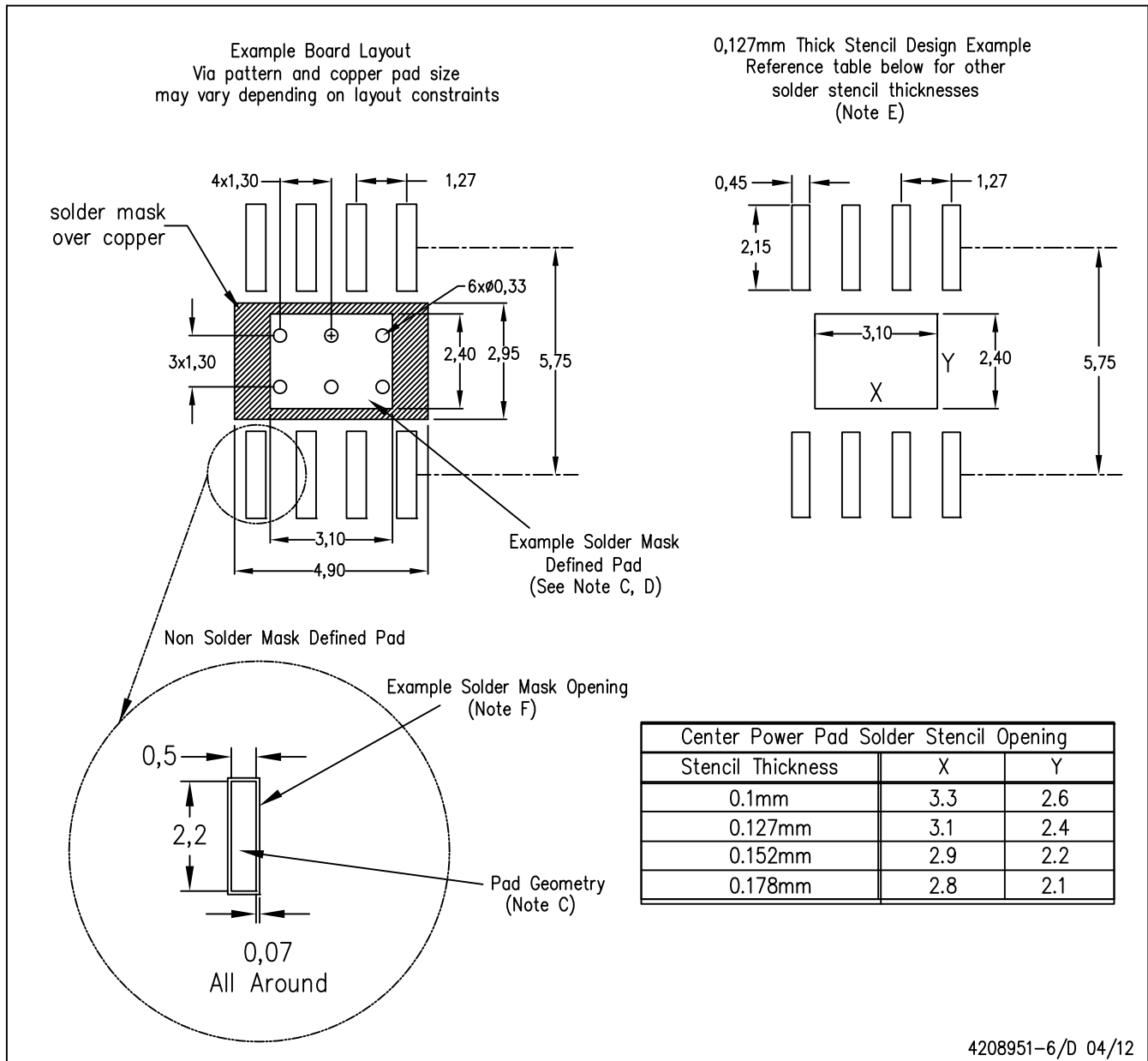
4206322-6/L 05/12

NOTE: A. All linear dimensions are in millimeters

PowerPAD is a trademark of Texas Instruments

DDA (R-PDSO-G8)

PowerPAD™ PLASTIC SMALL OUTLINE



- NOTES:
- All linear dimensions are in millimeters.
 - This drawing is subject to change without notice.
 - Publication IPC-7351 is recommended for alternate designs.
 - This package is designed to be soldered to a thermal pad on the board. Refer to Technical Brief, PowerPAD Thermally Enhanced Package, Texas Instruments Literature No. SLMA002, SLMA004, and also the Product Data Sheets for specific thermal information, via requirements, and recommended board layout. These documents are available at www.ti.com <<http://www.ti.com>>. Publication IPC-7351 is recommended for alternate designs.
 - Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Example stencil design based on a 50% volumetric metal load solder paste. Refer to IPC-7525 for other stencil recommendations.
 - Customers should contact their board fabrication site for solder mask tolerances between and around signal pads.

PowerPAD is a trademark of Texas Instruments.

重要声明和免责声明

TI 均以“原样”提供技术性 & 可靠性数据（包括数据表）、设计资源（包括参考设计）、应用或其他设计建议、网络工具、安全信息和其他资源，不保证其中不含任何瑕疵，且不做任何明示或暗示的担保，包括但不限于对适销性、适合某特定用途或不侵犯任何第三方知识产权的暗示担保。

所述资源可供专业开发人员应用 TI 产品进行设计使用。您将对以下行为独自承担全部责任：(1) 针对您的应用选择合适的 TI 产品；(2) 设计、验证并测试您的应用；(3) 确保您的应用满足相应标准以及任何其他安全、安保或其他要求。所述资源如有变更，恕不另行通知。TI 对您使用所述资源的授权仅限于开发资源所涉及 TI 产品的相关应用。除此之外不得复制或展示所述资源，也不提供其它 TI 或任何第三方的知识产权授权许可。如因使用所述资源而产生任何索赔、赔偿、成本、损失及债务等，TI 对此概不负责，并且您须赔偿由此对 TI 及其代表造成的损害。

TI 所提供产品均受 TI 的销售条款 (<http://www.ti.com.cn/zh-cn/legal/termsofsale.html>) 以及 [ti.com.cn](http://www.ti.com.cn) 上或随附 TI 产品提供的其他可适用条款的约束。TI 提供所述资源并不扩展或以其他方式更改 TI 针对 TI 产品所发布的可适用的担保范围或担保免责声明。

邮寄地址：上海市浦东新区世纪大道 1568 号中建大厦 32 楼，邮政编码：200122
Copyright © 2020 德州仪器半导体技术（上海）有限公司