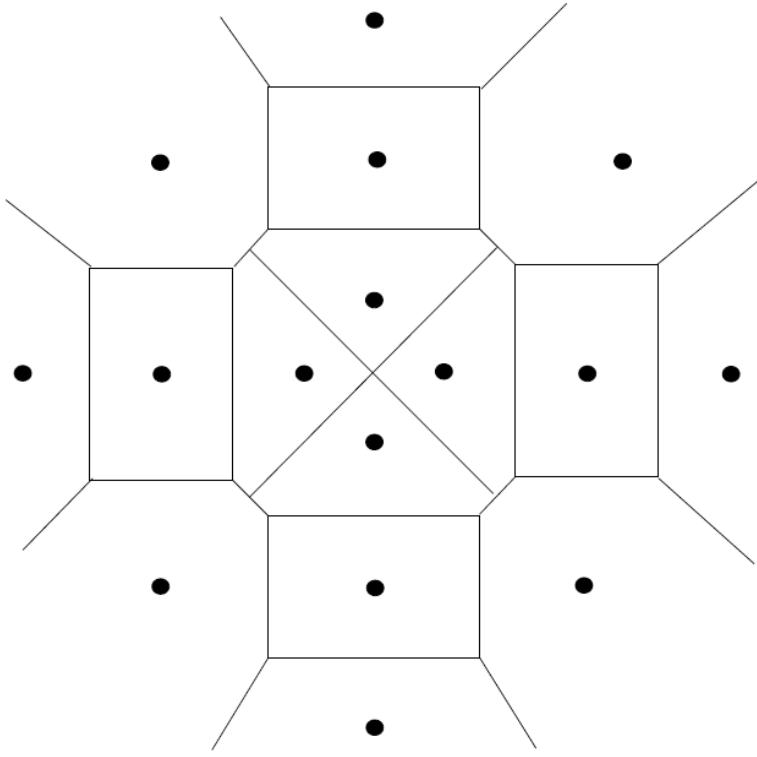
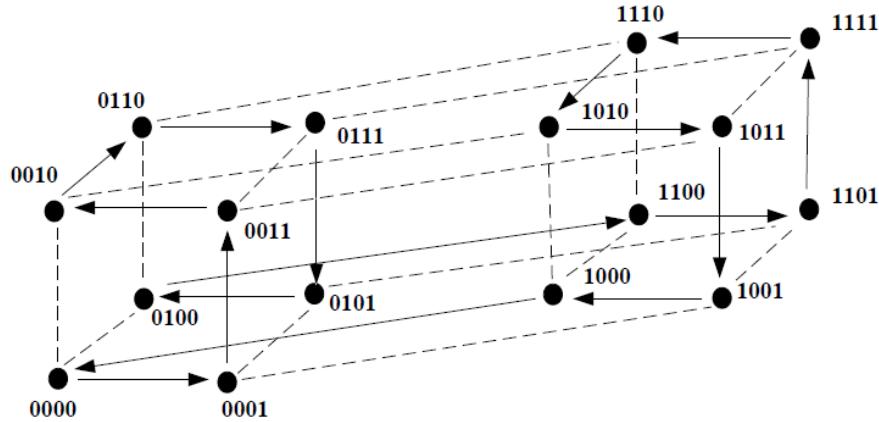


Problem 8.29

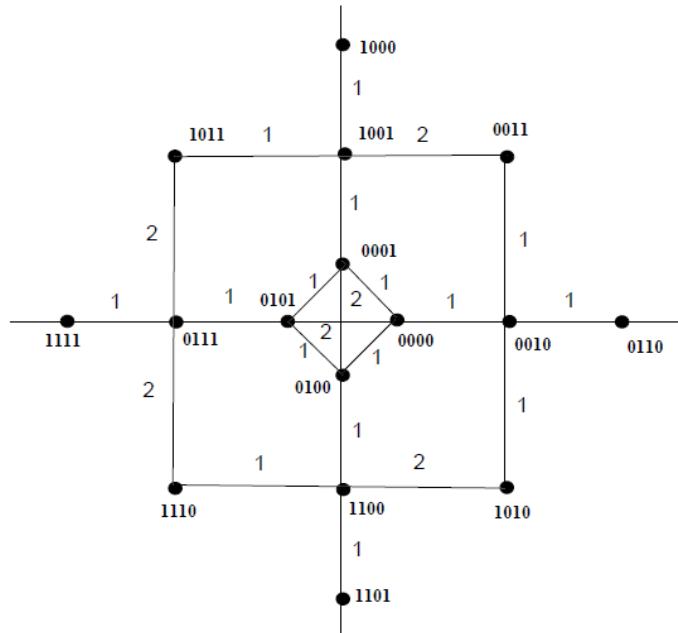
The optimum decision boundary of a point is determined by the perpendicular bisectors of each line segment connecting the point with its neighbors. The decision regions for the V.29 constellation are depicted in the next figure.

**Problem 8.30**

The following figure depicts a 4-cube and the way that one can traverse it in Gray-code order (see John F. Wakerly, Digital Design Principles and Practices, Prentice Hall, 1990). Adjacent points are connected with solid or dashed lines.



One way to label the points of the V.29 constellation using the Gray-code is depicted in the next figure. Note that the maximum Hamming distance between points with distance between them as large as 3 is only 2. Having labeled the innermost points, all the adjacent nodes can be found using the previous figure.



Problem 8.32

1) Although it is possible to assign three bits to each point of the 8-PSK signal constellation so that adjacent points differ in only one bit, this is not the case for the 8-QAM constellation of Figure P-10.12. This is because there are fully connected graphs consisted of three points. To see this consider an equilateral triangle with vertices A, B and C. If, without loss of generality, we assign the all zero sequence $\{0, 0, \dots, 0\}$ to point A, then point B and C should have the form

$$B = \{0, \dots, 0, 1, 0, \dots, 0\} \quad C = \{0, \dots, 0, 1, 0, \dots, 0\}$$

where the position of the 1 in the sequences is not the same, otherwise $B=C$. Thus, the sequences of B and C differ in two bits.

2) Since each symbol conveys 3 bits of information, the resulted symbol rate is

$$R_s = \frac{90 \times 10^6}{3} = 30 \times 10^6 \text{ symbols/sec}$$

3) The probability of error for an M-ary PSK signal is

$$P_M = 2Q\left[\sqrt{\frac{2E_s}{N_0}} \sin \frac{\pi}{M}\right]$$

whereas the probability of error for an M-ary QAM signal is upper bounded by

$$P_M = 4Q\left[\sqrt{\frac{3E_{av}}{(M-1)N_0}}\right]$$

Since, the probability of error is dominated by the argument of the Q function, the two signals will achieve the same probability of error if

$$\sqrt{2\text{SNR}_{\text{PSK}}} \sin \frac{\pi}{M} = \sqrt{\frac{3\text{SNR}_{\text{QAM}}}{M-1}}$$

With $M = 8$ we obtain

$$\sqrt{2\text{SNR}_{\text{PSK}}} \sin \frac{\pi}{8} = \sqrt{\frac{3\text{SNR}_{\text{QAM}}}{7}} \Rightarrow \frac{\text{SNR}_{\text{PSK}}}{\text{SNR}_{\text{QAM}}} = \frac{3}{7 \times 2 \times 0.3827^2} = 1.4627$$

4) Assuming that the magnitude of the signal points is detected correctly, then the detector for the 8-PSK signal will make an error if the phase error (magnitude) is greater than 22.5° . In the case of the 8-QAM constellation an error will be made if the magnitude phase error exceeds 45° . Hence, the QAM constellation is more immune to phase errors.

Problem 8.39

The vector $\mathbf{r} = [r_1, r_2]$ at the output of the integrators is

$$\mathbf{r} = [r_1, r_2] = [\int_0^{1.5} r(t)dt, \int_1^2 r(t)dt]$$

If $s_1(t)$ is transmitted, then

$$\begin{aligned}\int_0^{1.5} r(t)dt &= \int_0^{1.5} [s_1(t) + n(t)]dt = 1 + \int_0^{1.5} n(t)dt \\ &= 1 + n_1 \\ \int_1^2 r(t)dt &= \int_1^2 [s_1(t) + n(t)]dt = \int_1^2 n(t)dt \\ &= n_2\end{aligned}$$

where n_1 is a zero-mean Gaussian random variable with variance

$$\sigma_{n_1}^2 = E \left[\int_0^{1.5} \int_0^{1.5} n(\tau) n(v) d\tau dv \right] = \frac{N_0}{2} \int_0^{1.5} d\tau = 1.5$$

and n_2 is a zero-mean Gaussian random variable with variance

$$\sigma_{n_2}^2 = E \left[\int_1^2 \int_1^2 n(\tau) n(v) d\tau dv \right] = \frac{N_0}{2} \int_1^2 d\tau = 1$$

Thus, the vector representation of the received signal (at the output of the integrators) is

$$\mathbf{r} = [1 + n_1, n_2]$$

Similarly we find that if $s_2(t)$ is transmitted, then

$$\mathbf{r} = [0.5 + n_1, 1 + n_2]$$

Suppose now that the detector bases its decisions on the rule

$$\begin{matrix} s_1 \\ r_1 - r_2 & \begin{matrix} > \\ < \end{matrix} & T \\ s_2 \end{matrix}$$

The probability of error $P(e|s_1)$ is obtained as

$$\begin{aligned}P(e|s_1) &= P(r_1 - r_2 < T | s_1) \\ &= P(1 + n_1 - n_2 < T) = P(n_1 - n_2 < T - 1) \\ &= P(n < T)\end{aligned}$$

where the random variable $n = n_1 - n_2$ is zero-mean Gaussian with variance

$$\begin{aligned}\sigma_n^2 &= \sigma_{n_1}^2 + \sigma_{n_2}^2 - 2E[n_1 n_2] \\ &= \sigma_{n_1}^2 + \sigma_{n_2}^2 - 2 \int_1^{1.5} \frac{N_0}{2} d\tau \\ &= 1.5 + 1 - 2 \times 0.5 = 1.5\end{aligned}$$

Hence,

$$P(e|s_1) = \frac{1}{\sqrt{2\pi\sigma_n^2}} \int_{-\infty}^{T-1} e^{-\frac{x^2}{2\sigma_n^2}} dx$$

Similarly we find that

$$\begin{aligned}P(e|s_2) &= P(0.5 + n_1 - 1 - n_2 > T) \\ &= P(n_1 - n_2 > T + 0.5) \\ &= \frac{1}{\sqrt{2\pi\sigma_n^2}} \int_{T+0.5}^{\infty} e^{-\frac{x^2}{2\sigma_n^2}} dx\end{aligned}$$

The average probability of error is

$$\begin{aligned}P(e) &= \frac{1}{2}P(e|s_1) + \frac{1}{2}P(e|s_2) \\ &= \frac{1}{2\sqrt{2\pi\sigma_n^2}} \int_{-\infty}^{T-1} e^{-\frac{x^2}{2\sigma_n^2}} dx + \frac{1}{2\sqrt{2\pi\sigma_n^2}} \int_{T+0.5}^{\infty} e^{-\frac{x^2}{2\sigma_n^2}} dx\end{aligned}$$

To find the value of T that minimizes the probability of error, we set the derivative of $P(e)$ with respect to T equal to zero. Using the Leibnitz rule for the differentiation of definite integrals, we obtain

$$\frac{\partial P(e)}{\partial T} = \frac{1}{2\sqrt{2\pi\sigma_n^2}} \left[e^{-\frac{(T-1)^2}{2\sigma_n^2}} - e^{-\frac{(T+0.5)^2}{2\sigma_n^2}} \right] = 0$$

or

$$(T-1)^2 = (T+0.5)^2 \Rightarrow T = 0.25$$

Thus, the optimal decision rule is

$$r_1 - r_2 \stackrel{s_1}{>} 0.25$$

Problem 12.5

$$\begin{aligned} H(X, Y) &= H(X, g(X)) = H(X) + H(g(X)|X) \\ &= H(g(X)) + H(X|g(X)) \end{aligned}$$

But, $H(g(X)|X) = 0$, since $g(\cdot)$ is deterministic. Therefore,

$$H(X) = H(g(X)) + H(X|g(X))$$

Since each term in the previous equation is non-negative we obtain

$$H(X) \geq H(g(X))$$

Equality holds when $H(X|g(X)) = 0$. This means that the values $g(X)$ uniquely determine X , or that $g(\cdot)$ is a one to one mapping.

Problem 12.13

1. The marginal distribution $P(x)$ is given by $P(x) = \sum_y P(x, y)$. Hence,

$$\begin{aligned} H(X) &= -\sum_x P(x) \log P(x) = -\sum_x \sum_y P(x, y) \log P(x) \\ &= -\sum_{x,y} P(x, y) \log P(x) \end{aligned}$$

Similarly it is proved that $H(Y) = -\sum_{x,y} P(x, y) \log P(y)$.

2. Using the inequality $\ln w \leq w - 1$ with $w = \frac{P(x)P(y)}{P(x,y)}$, we obtain

$$\ln \frac{P(x)P(y)}{P(x,y)} \leq \frac{P(x)P(y)}{P(x,y)} - 1$$

Multiplying the previous by $P(x, y)$ and adding over x, y , we obtain

$$\sum_{x,y} P(x, y) \ln P(x)P(y) - \sum_{x,y} P(x, y) \ln P(x, y) \leq \sum_{x,y} P(x)P(y) - \sum_{x,y} P(x, y) = 0$$

Hence,

$$\begin{aligned} H(X, Y) &\leq -\sum_{x,y} P(x, y) \ln P(x)P(y) = -\sum_{x,y} P(x, y) (\ln P(x) + \ln P(y)) \\ &= -\sum_{x,y} P(x, y) \ln P(x) - \sum_{x,y} P(x, y) \ln P(y) = H(X) + H(Y) \end{aligned}$$

Equality holds when $\frac{P(x)P(y)}{P(x,y)} = 1$, i.e when X, Y are independent.

Problem 12.14

$$H(X, Y) = H(X) + H(Y|X) = H(Y) + H(X|Y)$$

Also, from part 2., $H(X, Y) \leq H(X) + H(Y)$. Combining the two relations, we obtain

$$H(Y) + H(X|Y) \leq H(X) + H(Y) \implies H(X|Y) \leq H(X)$$

Suppose now that the previous relation holds with equality. Then,

$$-\sum_x P(x) \log P(x|y) = -\sum_x P(x) \log P(x) \Rightarrow \sum_x P(x) \log \left(\frac{P(x)}{P(x|y)} \right) = 0$$

However, $P(x)$ is always greater or equal to $P(x|y)$, so that $\log(P(x)/P(x|y))$ is non-negative. Since $P(x) > 0$, the above equality holds if and only if $\log(P(x)/P(x|y)) = 0$ or equivalently if and only if $P(x)/P(x|y) = 1$. This implies that $P(x|y) = P(x)$ meaning that X and Y are independent.

Problem 12.46

The capacity of the additive white Gaussian channel is :

$$C = \frac{1}{2} \log \left(1 + \frac{P}{N_0 W} \right)$$

For the nonwhite Gaussian noise channel, although the noise power is equal to the noise power in the white Gaussian noise channel, the capacity is higher, The reason is that since noise samples are correlated, knowledge of the previous noise samples provides partial information on the future noise samples and therefore reduces their effective variance.

12.6.

$$H(X) = \sum_{i=1}^6 P_i \log_2 \frac{1}{P_i} = 2.4087 \text{ bits/sample}$$

$$f = 2 \times 6000 + 2000 = 14000 \text{ Hz}$$

$$H(X) = 2.4087 \times 14000 = 33721.8 \text{ bits/sec}$$

12.32.

$$(1) \quad H(X) = p \log_2 \frac{1}{p} + (1-p) \log_2 \frac{1}{1-p}$$

$$H(Y) = (1+2\varepsilon p - \varepsilon - p) \log_2 \frac{1}{1+2\varepsilon p - \varepsilon - p} + (\varepsilon + p - 2\varepsilon p) \log_2 \frac{1}{\varepsilon + p - 2\varepsilon p}$$

$$H(Y|X) = \varepsilon \log_2 \frac{1}{\varepsilon} + (1-\varepsilon) \log_2 \frac{1}{1-\varepsilon}$$

$$H(X, Y) = p \log_2 \frac{1}{p} + (1-p) \log_2 \frac{1}{1-p} + \varepsilon \log_2 \frac{1}{\varepsilon} + (1-\varepsilon) \log_2 \frac{1}{1-\varepsilon}$$

$$H(X|Y) = H(X, Y) - H(Y)$$

$$I(X; Y) = H(Y) - H(Y|X) = (1+2\varepsilon p - \varepsilon - p) \log_2 \frac{1}{1+2\varepsilon p - \varepsilon - p} + (\varepsilon + p - 2\varepsilon p) \log_2 \frac{1}{\varepsilon + p - 2\varepsilon p} \\ - \varepsilon \log_2 \frac{1}{\varepsilon} - (1-\varepsilon) \log_2 \frac{1}{1-\varepsilon}$$

$$(2) \quad \max I(X; Y) = \max H(Y)$$

$$P(Y=1) = P(Y=0) = \frac{1}{2}$$

$$\therefore P = \frac{1}{2}$$

(3) $\min I(X; Y) \Rightarrow X \text{ and } Y \text{ are independent.}$

$$\begin{cases} P(X=0, Y=0) = P(X=0)P(Y=0) \\ P(X=0, Y=1) = P(X=0)P(Y=1) \\ P(X=1, Y=0) = P(X=1)P(Y=0) \\ P(X=1, Y=1) = P(X=1)P(Y=1) \end{cases} \quad \therefore \varepsilon = \frac{1}{2}$$

12.36.

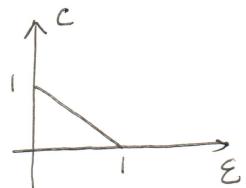
$$P(X) = \begin{cases} P & X=0 \\ 1-P & X=1 \end{cases}$$

$$C = \max \{ I(X; Y) \} = \max \{ H(Y) - H(Y|X) \}$$

$$H(Y) = p(1-\varepsilon) \log_2 \frac{1}{p(1-\varepsilon)} + (1-p)(1-\varepsilon) \log_2 \frac{1}{(1-p)(1-\varepsilon)} + \varepsilon \log_2 \frac{1}{\varepsilon}$$

$$H(Y|X) = p H(Y|X=0) + (1-p) H(Y|X=1) = p H(\varepsilon) + (1-p) H(\varepsilon)$$

$$C = \max \{ H(Y) - H(Y|X) \} = (1-\varepsilon) H(p) = 1-\varepsilon$$





9.9.

$$s_1(t) = \sqrt{\frac{2E_s}{T}} \cos(2\pi f_c t)$$

$$s_2(t) = \sqrt{\frac{2E_s}{T}} \cos(2\pi f_c t + 2\pi \Delta f t)$$

$$P_{12} = \frac{1}{E_s} \int_0^T s_1(t) s_2(t) dt = \frac{1}{T} \left[\int_0^T \cos(2\pi \Delta f t) dt + \int_0^T \cos(4\pi f_c t + 2\pi \Delta f t) dt \right]$$

$$\therefore f_c \gg \frac{1}{T}$$

$$\therefore P_{12} = \frac{1}{T} \int_0^T \cos(2\pi \Delta f t) dt = \frac{\sin(2\pi \Delta f T)}{2\pi \Delta f T}$$

$$\frac{dP_{12}}{dt} = \frac{2\pi \Delta f \cdot \cos(2\pi \Delta f t) \cdot 2\pi \Delta f t - \sin(2\pi \Delta f t) \cdot 2\pi \Delta f}{(2\pi \Delta f t)^2} = 0$$

$$2\pi \Delta f T = \tan(2\pi \Delta f T)$$

$$2\pi \Delta f T = 4.4934$$

$$\Delta f = \frac{0.7151}{T}$$

$$\cos \theta_{12} = -0.2172$$

$$d_{12}^2 = \|s_1\|^2 + \|s_2\|^2 - 2\|s_1\|\|s_2\| \cos \theta_{12} = 2E_s(1 - \cos \theta_{12})$$

$$P_e = Q\left(\sqrt{\frac{d_{12}^2}{2N_0}}\right) = Q\left(\sqrt{\frac{1.2172E_s}{N_0}}\right)$$

9.10.

$$(1) r(t) = \sqrt{\frac{2E_s}{T}} \cos(2\pi f_c t + \phi_m) + n(t)$$

$$r_m = \int_0^T r(t) \cos(2\pi f_c t + 2\pi m \Delta f t + \hat{\phi}_m) dt$$

$$= \sqrt{\frac{2E_s}{T}} \cdot \frac{1}{2} \int_0^T \cos(2\pi m \Delta f t + \hat{\phi}_m - \phi_m) dt + n \quad n \sim N(0, \frac{N_0}{2})$$

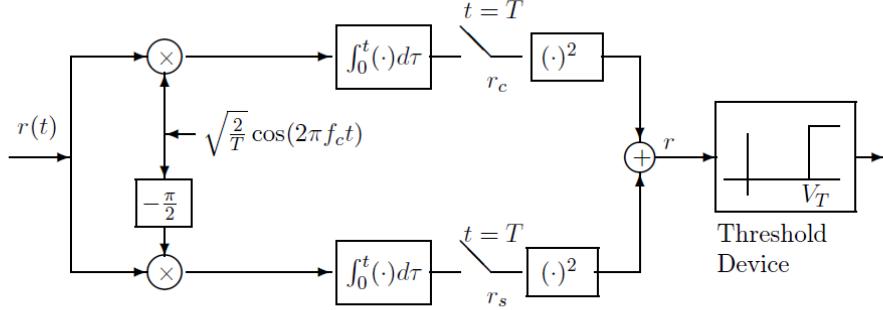
$$(2) \int_0^T \cos(2\pi m \Delta f t + \hat{\phi}_m - \phi_m) dt = 0$$

$$m \Delta f = n \cdot \frac{1}{T}$$

$$\therefore (\Delta f)_{\min} = \frac{1}{T}$$

Problem 9.12

1. The noncoherent envelope detector for the on-off keying signal is depicted in the next figure.



2. If $s_0(t)$ is sent, then the received signal is $r(t) = n(t)$ and therefore the sampled outputs r_c , r_s are zero-mean independent Gaussian random variables with variance $\frac{N_0}{2}$. Hence, the random variable $r = \sqrt{r_c^2 + r_s^2}$ is Rayleigh distributed and the PDF is given by :

$$p(r|s_0(t)) = \frac{r}{\sigma^2} e^{-\frac{r^2}{2\sigma^2}} = \frac{2r}{N_0} e^{-\frac{r^2}{N_0}}$$

If $s_1(t)$ is transmitted, then the received signal is :

$$r(t) = \sqrt{\frac{2\mathcal{E}_b}{T_b}} \cos(2\pi f_c t + \phi) + n(t)$$

Crosscorrelating $r(t)$ by $\sqrt{\frac{2}{T}} \cos(2\pi f_c t)$ and sampling the output at $t = T$, results in

$$\begin{aligned} r_c &= \int_0^T r(t) \sqrt{\frac{2}{T}} \cos(2\pi f_c t) dt \\ &= \int_0^T \frac{2\sqrt{\mathcal{E}_b}}{T_b} \cos(2\pi f_c t + \phi) \cos(2\pi f_c t) dt + \int_0^T n(t) \sqrt{\frac{2}{T}} \cos(2\pi f_c t) dt \\ &= \frac{2\sqrt{\mathcal{E}_b}}{T_b} \int_0^T \frac{1}{2} (\cos(2\pi 2f_c t + \phi) + \cos(\phi)) dt + n_c \\ &= \sqrt{\mathcal{E}_b} \cos(\phi) + n_c \end{aligned}$$

where n_c is zero-mean Gaussian random variable with variance $\frac{N_0}{2}$. Similarly, for the quadrature component we have :

$$r_s = \sqrt{\mathcal{E}_b} \sin(\phi) + n_s$$

The PDF of the random variable $r = \sqrt{r_c^2 + r_s^2} = \sqrt{\mathcal{E}_b + n_c^2 + n_s^2}$ follows the Rician distribution :

$$p(r|s_1(t)) = \frac{r}{\sigma^2} e^{-\frac{r^2+\mathcal{E}_b}{2\sigma^2}} I_0\left(\frac{r\sqrt{\mathcal{E}_b}}{\sigma^2}\right) = \frac{2r}{N_0} e^{-\frac{r^2+\mathcal{E}_b}{N_0}} I_0\left(\frac{2r\sqrt{\mathcal{E}_b}}{N_0}\right)$$

3. For equiprobable signals the probability of error is given by:

$$P(\text{error}) = \frac{1}{2} \int_{-\infty}^{V_T} p(r|s_1(t)) dr + \frac{1}{2} \int_{V_T}^{\infty} p(r|s_0(t)) dr$$

Since $r > 0$ the expression for the probability of error takes the form

$$\begin{aligned} P(\text{error}) &= \frac{1}{2} \int_0^{V_T} p(r|s_1(t))dr + \frac{1}{2} \int_{V_T}^{\infty} p(r|s_0(t))dr \\ &= \frac{1}{2} \int_0^{V_T} \frac{r}{\sigma^2} e^{-\frac{r^2+\mathcal{E}_b}{2\sigma^2}} I_0\left(\frac{r\sqrt{\mathcal{E}_b}}{\sigma^2}\right) dr + \frac{1}{2} \int_{V_T}^{\infty} \frac{r}{\sigma^2} e^{-\frac{r^2}{2\sigma^2}} dr \end{aligned}$$

The optimum threshold level is the value of V_T that minimizes the probability of error. However, when $\frac{\mathcal{E}_b}{N_0} \gg 1$ the optimum value is close to: $\frac{\sqrt{\mathcal{E}_b}}{2}$ and we will use this threshold to simplify the analysis. The integral involving the Bessel function cannot be evaluated in closed form. Instead of $I_0(x)$ we will use the approximation :

$$I_0(x) \approx \frac{e^x}{\sqrt{2\pi x}}$$

which is valid for large x , that is for high SNR. In this case :

$$\frac{1}{2} \int_0^{V_T} \frac{r}{\sigma^2} e^{-\frac{r^2+\mathcal{E}_b}{2\sigma^2}} I_0\left(\frac{r\sqrt{\mathcal{E}_b}}{\sigma^2}\right) dr \approx \frac{1}{2} \int_0^{\frac{\sqrt{\mathcal{E}_b}}{2}} \sqrt{\frac{r}{2\pi\sigma^2\sqrt{\mathcal{E}_b}}} e^{-(r-\sqrt{\mathcal{E}_b})^2/2\sigma^2} dr$$

This integral is further simplified if we observe that for high SNR, the integrand is dominant in the vicinity of $\sqrt{\mathcal{E}_b}$ and therefore, the lower limit can be substituted by $-\infty$. Also

$$\sqrt{\frac{r}{2\pi\sigma^2\sqrt{\mathcal{E}_b}}} \approx \sqrt{\frac{1}{2\pi\sigma^2}}$$

and therefore :

$$\begin{aligned} \frac{1}{2} \int_0^{\frac{\sqrt{\mathcal{E}_b}}{2}} \sqrt{\frac{r}{2\pi\sigma^2\sqrt{\mathcal{E}_b}}} e^{-(r-\sqrt{\mathcal{E}_b})^2/2\sigma^2} dr &\approx \frac{1}{2} \int_{-\infty}^{\frac{\sqrt{\mathcal{E}_b}}{2}} \sqrt{\frac{1}{2\pi\sigma^2}} e^{-(r-\sqrt{\mathcal{E}_b})^2/2\sigma^2} dr \\ &= \frac{1}{2} Q\left[\sqrt{\frac{\mathcal{E}_b}{2N_0}}\right] \end{aligned}$$

Finally :

$$\begin{aligned} P(\text{error}) &= \frac{1}{2} Q\left[\sqrt{\frac{\mathcal{E}_b}{2N_0}}\right] + \frac{1}{2} \int_{\frac{\sqrt{\mathcal{E}_b}}{2}}^{\infty} \frac{2r}{N_0} e^{-\frac{r^2}{N_0}} dr \\ &\leq \frac{1}{2} Q\left[\sqrt{\frac{\mathcal{E}_b}{2N_0}}\right] + \frac{1}{2} e^{-\frac{\mathcal{E}_b}{4N_0}} \end{aligned}$$



9.9.

$$s_1(t) = \sqrt{\frac{2E_s}{T}} \cos(2\pi f_c t)$$

$$s_2(t) = \sqrt{\frac{2E_s}{T}} \cos(2\pi f_c t + 2\pi \Delta f t)$$

$$P_{12} = \frac{1}{E_s} \int_0^T s_1(t) s_2(t) dt = \frac{1}{T} \left[\int_0^T \cos(2\pi \Delta f t) dt + \int_0^T \cos(4\pi f_c t + 2\pi \Delta f t) dt \right]$$

$$\therefore f_c \gg \frac{1}{T}$$

$$\therefore P_{12} = \frac{1}{T} \int_0^T \cos(2\pi \Delta f t) dt = \frac{\sin(2\pi \Delta f T)}{2\pi \Delta f T}$$

$$\frac{dP_{12}}{dt} = \frac{2\pi \Delta f \cdot \cos(2\pi \Delta f t) \cdot 2\pi \Delta f t - \sin(2\pi \Delta f t) \cdot 2\pi \Delta f}{(2\pi \Delta f t)^2} = 0$$

$$2\pi \Delta f T = \tan(2\pi \Delta f T)$$

$$2\pi \Delta f T = 4.4934$$

$$\Delta f = \frac{0.7151}{T}$$

$$\cos \theta_{12} = -0.2172$$

$$d_{12}^2 = \|s_1\|^2 + \|s_2\|^2 - 2\|s_1\|\|s_2\| \cos \theta_{12} = 2E_s(1 - \cos \theta_{12})$$

$$P_e = Q\left(\sqrt{\frac{d_{12}^2}{2N_0}}\right) = Q\left(\sqrt{\frac{1.2172E_s}{N_0}}\right)$$

9.10.

$$(1) r(t) = \sqrt{\frac{2E_s}{T}} \cos(2\pi f_c t + \phi_m) + n(t)$$

$$r_m = \int_0^T r(t) \cos(2\pi f_c t + 2\pi m \Delta f t + \hat{\phi}_m) dt$$

$$= \sqrt{\frac{2E_s}{T}} \cdot \frac{1}{2} \int_0^T \cos(2\pi m \Delta f t + \hat{\phi}_m - \phi_m) dt + n \quad n \sim N(0, \frac{N_0}{2})$$

$$(2) \int_0^T \cos(2\pi m \Delta f t + \hat{\phi}_m - \phi_m) dt = 0$$

$$m \Delta f = n \cdot \frac{1}{T}$$

$$\therefore (\Delta f)_{\min} = \frac{1}{T}$$

13.5.

Let the parity check matrix $\vec{H} = [\vec{h}_1, \dots, \vec{h}_n]$ and the linear block codeword $\vec{C} = [c_1, \dots, c_n]$, with nonzero elements c_{i1}, \dots, c_{il}

$$\therefore \vec{C}\vec{H} = c_1\vec{h}_1 + \dots + c_n\vec{h}_n = c_{i1}\vec{h}_{i1} + \dots + c_{il}\vec{h}_{il} = 0$$

$$\therefore \vec{h}_{i1} + \dots + \vec{h}_{il} = 0$$

\therefore the minimum number of columns of H that are dependent = l_{\min}

Let the minimum number of columns of H that are dependent is d_{\min} .

$$\vec{C}\vec{H} = c_1\vec{h}_1 + \dots + c_n\vec{h}_n = c_1\vec{h}_{i1} + \dots + c_{d_{\min}}\vec{h}_{i d_{\min}} = 0$$

\therefore the minimum Hamming distance = d_{\min} .

For Hamming code, $\forall h_i + h_j = h_m \in H \Rightarrow h_i + h_j + h_m = 0$

$$\therefore d_{\min} = 3$$

13.9.

c_1, \dots, c_{16} are Hamming codewords in P_{15} of lec 10.

$$\begin{bmatrix} c_1 & c_2 & \dots & c_{16} \\ e_1 & e_1 \oplus c_2 & \dots & e_1 \oplus c_{16} \\ \vdots & \vdots & & \vdots \\ e_7 & e_7 \oplus c_2 & \dots & e_7 \oplus c_{16} \end{bmatrix} \begin{array}{l} 0 \\ e_1 H^T \\ \vdots \\ e_7 H^T \end{array} \text{ Syndrome.}$$

$$r = [1110100] \quad s = r H^T = [110]$$

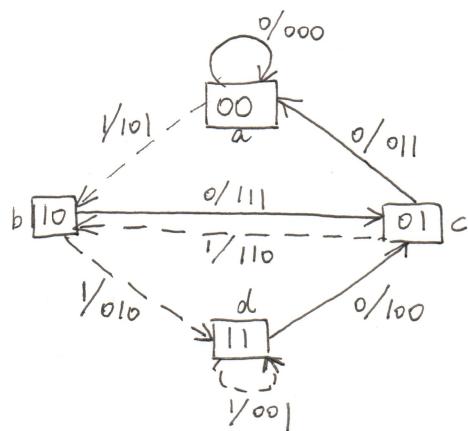
$$H^T = \begin{bmatrix} 1 & 1 & 0 \\ 0 & 1 & 1 \\ 1 & 1 & 1 \\ 1 & 0 & 1 \\ \hline 1 & 0 & 0 \\ 0 & 1 & 0 \\ 0 & 0 & 1 \end{bmatrix} \quad e = [1000000]$$

$$\therefore c = [0110100]$$

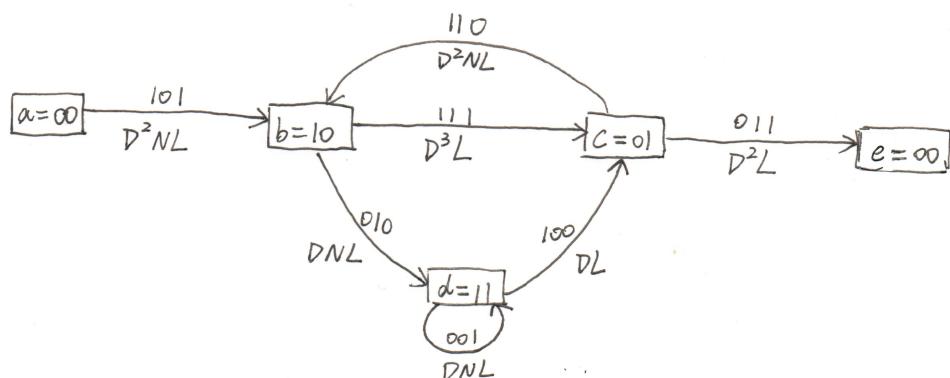
\therefore the message is 0110.

13. 13.

(1)



(2)

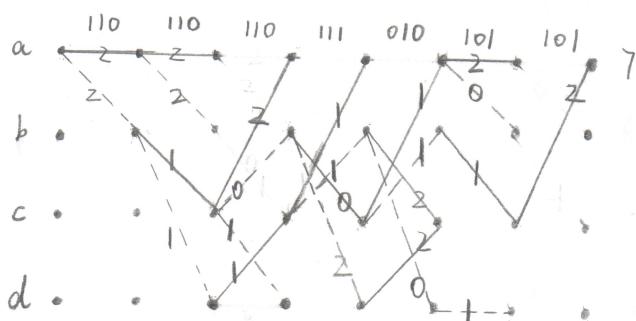


$$\begin{cases} X_b = D^2NL X_a + D^2NL X_c \\ X_c = D^3L X_b + DL X_d \\ X_d = DNL X_b + DNL X_d \\ X_e = D^2L X_c \end{cases}$$

$$T(D) = \frac{X_e}{X_a} = \frac{D^6N^2L^4 + D^7NL^3 - D^8N^2L^4}{1 - DNL - D^5NL^2 + D^6N^2L^3 - D^4N^2L^3}$$

(3) $d_{\text{free}} = 6$.

(4)



∴ decoding sequence is
 $\{101, 111, 110, 111, 110, 111, 011\}$
 information sequence is
 $\{10101\}$

$$(5) P_b \leq \left. \frac{\partial T_2(D, N)}{\partial N} \right|_{N=1, D=\sqrt{4p(1-p)}} \quad T_2(D, N) = T(D, N)|_{L=1} \approx D^6N^2$$

$$\approx \left. \frac{\partial D^6N^2}{\partial N} \right|_{N=1, D=\sqrt{4p(1-p)}} = 2(4p(1-p))^3$$

$$\therefore P_b \leq 1.28 \times 10^{-13}$$