

Classical Signal Chp 1 Impulse Functions	
Note: (n-n0) = shift right. (n+n0) = shift left	
	$\delta[n] = \begin{cases} 1, n=0 \\ 0, n \neq 0 \end{cases}$
	$u[n] = \begin{cases} 1, n \geq 0 \\ 0, n < 0 \end{cases}$
	$x[n] = a^n, 0 < a < 1$

Discrete Convolution	
<ul style="list-style-type: none"> $y[n] = x[n] * h[n] = \sum_k x[k]h[n-k] = \sum_k x[n-k]h[k] \rightarrow$ commutative 	
Discrete Time Systems	
<ul style="list-style-type: none"> Transformation T of input sequence x[n] into output sequence y[n] $y[n] = T(x[n])$ 	
Properties of Systems	
Stable	
<ul style="list-style-type: none"> Bounded input, bounded output: $\sum_n h[n] < \infty$ FIR filters: stable as long as values are finite \rightarrow finite sum of numbers are finite h[n] is bounded if $h[n] < B_h$ for all n. y[n] is bounded if $y[n] < B_y$ for all n System is stable if x[n] is bounded, then y[n] is also bounded 	
$y[n] = g(x)x[n] \rightarrow$ if g(n) bounded	$y[n] = x[n-n_0]$
$y[n] = x[n] + 3u[n+1] \rightarrow x[n] \leq B_x$ and $y[n] \leq B_x + 3u[n+1] \leq B_x + 3$	$y[n] = e^{x[n]}$ $ x[n] \leq B_x$ and $ y[n] \leq e^{B_x}$

Causal	
<ul style="list-style-type: none"> y[n] does not depend on future inputs, i.e. for $n > n_0 \rightarrow -\infty < n < \infty$ Output y[n] at time $n = n_0$ only depends on input x[n] at $n \leq n_0$ LTI system only: is causal only when $h[n] = 0$ for $n < 0$ 	
$y[n] = g(x)x[n]$	$y[n] = x[n-n_0]$
$y[n] = e^{x[n]}$	causal: $n-n_0 \leq n$, then $n_0 \geq 0$.
$y[n] = x[n] + 3u[n+1]$	not causal: $n-n_0 > n$, then $n_0 < 0$.

Linear	
<ul style="list-style-type: none"> If $T(ax_1[n] + bx_2[n]) = ay_1[n] + by_2[n]$, it is linear Linear combination of inputs = linear combination of corresponding outputs 	
$y[n] = g(x)x[n]$	$y[n] = e^{x[n]}$
$y[n] = x[n-n_0]$	$T(ax_1[n] + bx_2[n])$
$y[n] = x[n] + 3u[n+1]$	$= e^{ax_1[n] + bx_2[n]} \neq ay_1[n] + by_2[n]$

Time invariant	
<ul style="list-style-type: none"> $x_1[n-n_0] * h[n] = \sum_{k=-\infty}^{\infty} x_1[k-n_0]h[n-k] = \sum_{m=-\infty}^{\infty} x_1[m]h[n-n_0-m] = y_1[n-n_0]$ 	
$y[n] = g(x)x[n]$	$y[n] = x[n-n_0]$
$= g[n-n_0]x[n-n_0] = y[n-n_0]$	$y[n] = e^{x[n]}$
$y[n] = x[n] + 3u[n+1]$	$(x[n-n_0]) = x[n-n_0] + 3u[n+1] \neq y[n-n_0]$

Memoryless	
<ul style="list-style-type: none"> y[n] at any value of n depends on x[n] only at time n. Output considers present input only A special case of causal (if memoryless, always causal) 	
$y[n] = g(x)x[n]$	$y[n] = x[n-n_0]$
	Only if $n_0 = 0$, Memoryless.
$y[n] = e^{x[n]}$	$y[n] = x[n] + 3u[n+1]$
	y[n] at all values of n depends only on x[n] at time n.

Properties of LTI systems	
<ul style="list-style-type: none"> All LTI systems can be expressed with convolution with impulse h[n] To find h[n], set input $x[n] = \delta[n]$ and output $y[n] = h[n]$ 	
Geometric Series: $a_n = ar^{n-1}$	
<ul style="list-style-type: none"> Finite: $a^0 + a + ar^2 + \dots + ar^{n-1} = \frac{a(1-r^n)}{1-r}$ OR $\frac{a(r^n-1)}{r-1}$ where $r \neq 1$ Infinite: $a^0 + a^1 + ar^2 + ar^3 + \dots = \frac{a}{1-r}$ where $r < 1$ Infinite 2: $\sum_{k=m}^{\infty} ar^k = \frac{ar^m}{1-r}$ Variation (finite): $\sum_{k=N_1}^{N_2} a^k = \frac{a^{N_1}-a^{N_2+1}}{1-a}$ where $N_2 \geq N_1$ Variation (finite, complex): $\sum_{k=N_1}^{N_2} e^{j\omega k} = \frac{e^{j\omega(N_1-1)}-e^{j\omega(N_2+1)}}{1-e^{j\omega}}$ where $N_2 \geq N_1$ 	

Complex Numbers Identities		
Cartesian: $z = a + jb$	Polar: $z = z e^{j\varphi}$	$ z = \sqrt{a^2 + b^2}$
Euler: $e^{jx} = \cos x + jsinx \rightarrow \cos x = \frac{e^{jx} + e^{-jx}}{2} \rightarrow \sin x = \frac{e^{jx} - e^{-jx}}{2j}$		
Continuous / Discrete Time Fourier Transform		
CFT: $\int_{-\infty}^{\infty} x(t)e^{-j\Omega t} dt$		
Inverse CFT: $x(t) = \frac{1}{2\pi} \int_{-\infty}^{\infty} X(\Omega)e^{j\Omega t} d\Omega$		
DTFT: $X(e^{j\omega}) = \sum_{n=-\infty}^{\infty} x[n]e^{j\omega n}$		
Inverse DTFT: $x[n] = \frac{1}{2\pi} \int_{-\pi}^{\pi} X(e^{j\omega})e^{j\omega n} d\omega$		

Classical Signal Chp 2 Fourier Conversion	
Sequence	Fourier Transform
$\delta(n)$	1
$\delta(n-n_0)$ where $n_0 \in \mathbb{Z}$	$e^{-j\omega n_0} \rightarrow n_0$ is an integer
1 where $(-\infty < n < \infty)$	$\sum_{k=-\infty}^{\infty} 2\pi\delta(\omega + 2\pi k)$
$a^n u[n]$ where $(a < 1)$	$\frac{1}{1-ae^{-j\omega}}$
u[n]	$\frac{1}{1-e^{-j\omega}} + \sum_{k=-\infty}^{\infty} \pi\delta(\omega + 2\pi k)$
$(n+1)a^n u[n]$ where $(a < 1)$	$\frac{1}{(1-ae^{-j\omega})^2}$
$\frac{r^{sin\omega_p(n+1)}}{sin\omega_p} u[n]$ where $(r < 1)$	$\frac{1}{1-2r\cos\omega_p e^{-j\omega} + r^2 e^{-j2\omega}}$
$\frac{sin\omega_c n}{\pi n}$	$X(e^{j\omega}) = \begin{cases} 1, & \omega < \omega_c \\ 0, & \omega_c < \omega \leq \pi \end{cases}$
$x[n] = \begin{cases} 1, & 0 \leq n \leq M \\ 0, & otherwise \end{cases}$	$\frac{sin(\frac{\omega(M+1)}{2})}{sin(\frac{\omega}{2})} e^{j\frac{\omega M}{2}}$
$e^{j\omega_0 n}$	$\sum_{k=-\infty}^{\infty} 2\pi\delta(\omega - \omega_0 + 2\pi k)$
$cos(\omega_0 n + \phi)$	$\sum_{k=-\infty}^{\infty} [\pi e^{j\phi}\delta(\omega - \omega_0 + 2\pi k) + \pi e^{-j\phi}\delta(\omega + \omega_0 + 2\pi k)]$
Fourier Equations (Simplification)	
$\frac{1}{(1-ae^{-j\omega})(1-be^{-j\omega})} = \frac{a/(a-b)}{1-ae^{-j\omega}} - \frac{b/(a-b)}{1-be^{-j\omega}}$	

Properties of DTFT	
Linearity	$ax_1(n) + bx_2(n) \approx aX_1(e^{j\omega}) + bX_2(e^{j\omega})$
Time shift	$x(n-n_0) \approx e^{-j\omega n_0} X(e^{j\omega})$
Frequency Shift	$e^{j\omega n_0} x(n) \approx X(e^{j(\omega-\omega_0)})$
Convolution Theorem 1	$x(n) * h(n) \approx X(e^{j\omega})H(e^{j\omega}) = H(e^{j\omega})X(e^{j\omega})$
Theorem 2	$x(n)h(n) \approx X(e^{j\omega}) * H(e^{j\omega}) = \frac{1}{2\pi} \int_{-\pi}^{\pi} X(e^{j\theta})H(e^{j(\omega-\theta)})d\theta$ (if periodic, else is infinity)

Filters Frequency Response	
	Ideal Low-Pass Filter $H_{lp}(e^{j\omega}) = \begin{cases} 1, & \omega < \omega_c \\ 0, & \omega_c < \omega \leq \pi \end{cases}$
	Ideal High-Pass Filter $H_{hp}(e^{j\omega}) = \begin{cases} 0, & \omega < \omega_c \\ 1, & \omega_c < \omega \leq \pi \end{cases}$
	Ideal Band-stop Filter $H_{bs}(e^{j\omega}) = \begin{cases} 1, & \omega < \omega_a \\ 0, & \omega_a < \omega < \omega_b \\ 1, & \omega_b < \omega < \pi \end{cases}$
	Ideal Bandpass Filter $H_{bp}(e^{j\omega}) = \begin{cases} 0, & \omega < \omega_a \\ 1, & \omega_a < \omega < \omega_b \\ 0, & \omega_b < \omega < \pi \end{cases}$

**Find ω to prove filter Convert HP <-> LP : $H_{hp} = 1 - H_{lp}$ Convert BP <-> BS: $H_{bp} = 1 + H_{bs} \rightarrow$ made up of 2 LP Convert BS <-> HP: $H_{bs} = H_{hp} * H_{bsf}$	
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Filter Design by Windowing	
– Start with ideal frequency response $H(e^{j\omega}) \leftrightarrow h_l[n]$ – Multiply by window w[n] in time domain: $h_l[n]w[n]$ – Window shape and length M tradeoffs ringing and cutoff sharpness	

Classical Signal Chp 3	
Phase Distortion	
Consider ideal delay system: $h[n] = \delta[n-n_d]$ $H(e^{j\omega}) = e^{-j\omega n_d} \rightarrow H(e^{j\omega}) = 1 \rightarrow angle = -\omega n_d$	
Ideal filter with linear phase acceptable as filter without phase distortion	
<ul style="list-style-type: none"> E.g. ideal linear phase LPF: $H_{lp} = \begin{cases} e^{-j\omega\alpha}, & \omega < \omega_c, \alpha \in \mathbb{R} \\ 0, & \omega_c < \omega \leq \pi \end{cases}$ Generalised linear phase: $\omega\alpha + \beta$ 	
Type 1/2 FIR Linear Phase System	
Symmetric causal FIR $h[n] = \begin{cases} 0, & n < 0, n > M \\ h[M-n], & 0 \leq n \leq M \end{cases}$ even M: $H(e^{j\omega}) = \sum_{n=0}^M h[n]e^{-j\omega n} = e^{-j\omega M/2} \sum_{k=0}^{M/2} a[k]cos\omega k$ Where $a[0] = h[M/2]$ and $a[k] = 2h[(M/2) - k]$ Delay $\alpha = M/2$ (an integer) odd M: $H(e^{j\omega}) \sum_{n=0}^M h[n]e^{-j\omega n} = e^{-j\omega M/2} \sum_{k=0}^{(M+1)/2} b[k]cos(\omega(k-\frac{1}{2}))$ where $b[k] = 2h[(M+1)/2 - k]$ Delay $\alpha = M/2$ (an integer + half) Not Suitable for HPF and BSF because $H(e^{j\omega}) = 0$	
Kaiser Window	

$w[n] = \begin{cases} I_0\left(\beta\left(1-\left[\frac{n-M/2}{M/2}\right]^2\right)^{\frac{1}{2}}\right), & 0 \leq n \leq M \\ 0, & otherwise \end{cases}$		
Picking M and β for Kaiser Window		
$\beta = \begin{cases} 0.1102(A-8.7), & A > 50 \\ 0.5842(A-21)^{0.4} + 0.07886(A-21), & 21 \leq A \leq 50 \\ 0.0, & A < 21 \end{cases}$		
β controls shape of window: If $\beta = 0$, Kaiser window is rectangular window If β increases, Kaiser window looks more like Gaussian		
$M = \frac{A-8}{2.285\Delta\omega}$	$A = -20\log_{10} \delta$	For LP: $\Delta\omega = \omega_s - \omega_p$ For HP: $\Delta\omega = \omega_p - \omega_s$
$\omega_c = \frac{\omega_p + \omega_s}{2}$		
Finding magnitude: E.g. $0.95 < H(e^{j\omega}) < 1.05$ $Magnitude = \frac{Max + Min}{2} = \frac{0.95 + 1.05}{2}$		

We wish to use Kaiser window method to design a FIR filter with generalized linear phase that meets the following specifications: Mag = 1 $0.95 < H(e^{j\omega}) < 1.05$ H $0 \leq \omega \leq 0.2\pi$ Mag = 0 $ H(e^{j\omega}) < 0.1$ L $0.3\pi \leq \omega \leq 0.6\pi$ Mag = 1 $0.95 < H(e^{j\omega}) < 1.05$ H $0.7\pi \leq \omega \leq \pi$	
Find the Kaiser window parameters β and M so that the resulting windowed filter satisfies the above criteria. Justify your choice of δ and $\Delta\omega$. What is the frequency response of the ideal filter? $\delta = 0.05 \rightarrow$ because $\delta = 0.05$ is stricter than $\delta = 0.1$ in stopband $A = -20\log_{10} 0.05 = 26.0206$ $\beta = 0.5842(A-21)^{0.4} + 0.07886(A-21) = 1.5099$ $\Delta\omega_1 = 0.3\pi - 0.2\pi = 0.1\pi$ and $\Delta\omega_2 = 0.7\pi - 0.6\pi = 0.1\pi \rightarrow$ same value $M = \frac{A-8}{2.285\Delta\omega} = 25.1 \rightarrow$ round up $M = 26$	
$H_t(e^{j\omega}) = \begin{cases} e^{-j\omega M/2}, & 0 \leq \omega \leq \frac{0.2+0.3}{2}\pi \\ 0, & \frac{0.2+0.2}{2}\pi \leq \omega \leq \frac{0.6+0.7}{2}\pi \\ 2e^{j\omega M/2}, & \frac{0.6+0.7}{2}\pi \leq \omega \leq \pi \end{cases}$	
$= \begin{cases} e^{-j\omega M/2}, & 0 \leq \omega \leq 0.25\pi \\ 0, & 0.25\pi \leq \omega \leq 0.65\pi \\ 2e^{-j\omega M/2}, & 0.65\pi \leq \omega \leq \pi \end{cases}$	
Discrete Fourier Transform (DFT)	
– Sampled version of DTFT with sampling period $2\pi/N$ – Can be computed in N log N operations with FFT – Efficiently compute DTFT and convolutions	

Classical Signal Chp 4	
Wavelet Consider one cycle of the Spincycle transform illustrated. Suppose $x = [6 \ 12 \ 120 \ 116]$. What are the coefficients at location (a)-(j) in the spincycle, assuming we use the Haar transform, where $g = g_0 = \begin{bmatrix} \sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix}$, $h = \begin{bmatrix} -\sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix}$ and $h_0 = \begin{bmatrix} \sqrt{2} & -\sqrt{2} \\ 2 & 2 \end{bmatrix}$	
(a)	Required coefficient 1 = [116 6 12 120] \rightarrow shift right
(b)	Required coefficient 2 = [116 6 12 120] $\ast \begin{bmatrix} -\sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix} \rightarrow \downarrow 2$ $= \sqrt{2} \begin{bmatrix} 116-6 & 12-120 \\ 2 & 2 \end{bmatrix}$ $= \sqrt{2}[55 \ -54]$
(c)	Required coefficient 3i = $\sqrt{2}[55 \ 0 \ -54 \ 0]$ Final Required coefficient 3 = $\sqrt{2}[55 \ 0 \ -54 \ 0] \ast \begin{bmatrix} \sqrt{2} & -\sqrt{2} \\ 2 & 2 \end{bmatrix}$ $= \sqrt{2}\sqrt{2}[27.5 \ -27.5 \ -27 \ 27]$ $= [55 \ -55 \ -54 \ 54]$
(d)	Required coefficient 4 = [116 6 12 120] $\ast \begin{bmatrix} \sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix} \rightarrow \downarrow 2$ $= \sqrt{2} \begin{bmatrix} 116+6 & 12+120 \\ 2 & 2 \end{bmatrix}$ $= \sqrt{2}[61 \ 66]$
(e)	Required coefficient 5 = $\sqrt{2}[61 \ 66] \ast \begin{bmatrix} -\sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix} \rightarrow \downarrow 2$ $= \sqrt{2}\sqrt{2} \begin{bmatrix} 61-66 \\ 2 & 2 \end{bmatrix}$ $= [-5]$
(f)	Required coefficient 6 = [-5 0] $\ast \begin{bmatrix} \sqrt{2} & -\sqrt{2} \\ 2 & 2 \end{bmatrix}$ $= \sqrt{2}[-2.5 \ 2.5]$
(g)	Required coefficient 7 = $\sqrt{2}[61 \ 66] \ast \begin{bmatrix} \sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix} \rightarrow \downarrow 2$ $= \sqrt{2}\sqrt{2} \begin{bmatrix} 61+66 \\ 2 & 2 \end{bmatrix}$ $= [127]$
(h)	Required coefficient 8 = [127 0] $\ast \begin{bmatrix} \sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix}$ $= \sqrt{2}[63.5 \ 63.5]$
(i)	Required coefficient 9i = $\sqrt{2}[-2.5 \ 2.5] + \sqrt{2}[63.5 \ 63.5]$ $= \sqrt{2}[61 \ 66]$ Final Required coefficient 9 = $\sqrt{2}[61 \ 0 \ 66 \ 0] \ast \begin{bmatrix} \sqrt{2} & \sqrt{2} \\ 2 & 2 \end{bmatrix}$ $= \sqrt{2}\sqrt{2}[30.5 \ 30.5 \ 33 \ 33]$ $= [61 \ 61 \ 66 \ 66]$
(j)	Required coefficient 10i = [55 -55 -54 54] + [61 61 66 66] $= [116 \ 6 \ 12 \ 120]$ Final Required coefficient 10 = [6 12 120 116]

Statistical Chp 3 - Random walk	
$X_n: X_N = x_0 + \sum_{n=1}^N z_n$ x_0 : initial position $x_n = x_{n-1} + z_n$ for $n \geq 1$ $z_n = \pm 1$ with equal probability & Independent and Identically Distributed (i.i.d.) $p(x_n = k) = p\left(a = \frac{n+k}{2} \text{ heads in independent coin tosses}\right)$ $= \binom{n+k}{2} \frac{1}{2^n}$	
Markov Process: Random process is Markov if future and past conditionally independent given present Markov Chain: $p(x_0, \dots, x_{n-1}, x_n, x_{n+1}, \dots, x_N x_N)$ $= p(x_0, \dots, x_{n-1} x_n) p(x_{n+1}, \dots, x_N x_n)$ x_n : state at time n Transition Matrix: rows of T sum to 1	<p>3 state Markov chain example</p>

Markov Chain Properties	
Property (1): $\pi_{n+1} = \pi_n T$ where π_n is a row vector & $\pi_n(i) = p(x_n = s_i)$ $\pi_{n+1}(j) = p(x_{n+1} = s_j)$	
Property (2): Stationary Distribution $\pi_{n+1} = \pi_n T \rightarrow \pi_{n+2} = \pi_{n+1} T = \pi_n T^2 \rightarrow \dots \rightarrow \boxed{\pi_{n+k} = \pi_n T^k}$ Eigenvector (π^*): If $\pi^* = \pi^* T$, then π^* is stationary distri. of T where $\pi^* = 1$. Once we reach π^* , distribution of the state stays constant Fundamental Theorem of Markov Chain Satisfy: If all entries in $T^n > 0$ for all $n \geq 1$, fundamental theorem applies & T has a unique stationary distribution. E.g. (does not satisfy): (1) identity matrix: no unique stationary distribution. (2) Random walk: x_n does not satisfy the Fundamental Theorem. \rightarrow $p(x_{n0} = n_0 + 1) = 0$ (e.g., at time 5, there is zero probability of $x_5 = 6$).	

