

PTAT Current Drivers for Neural Stimulation

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Abstract—Overview of the design decisions for a PTAT current source and sink using 65nm TSMC PDK technology.

I. INTRODUCTION

THE complete system for neural stimulation is described in this report. Driver electronics must minimize loading effects due to the high-impedance of an implantable neural electrodes. This writeup discusses the method and implementation of maximum output impedance drivers, on the order of Gigaohms ($G\Omega$).

A. Objective

Continuing the design for the neural stimulation, a current source driver is designed including layout for all devices, and a physical switch. The accuracy of the current source is verified by integrating the positive and negative current pulses.

B. Top Level Schematic

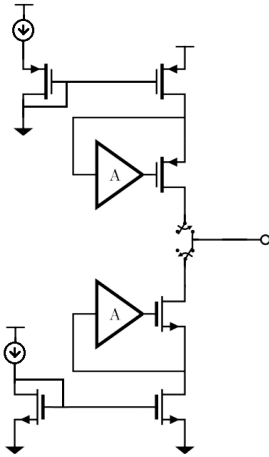


Fig. 1: Source and Sink Drivers with Gain-Boost

II. DESIGN

The gain boosted cascode is applied to both the source and sink drivers. PMOS devices are implemented in the source driver and NMOS devices in the sink driver. The source operates from V_{DD} to the electrode voltage and the sink operates from the electrode voltage to ground. The R_{out} is defined as

$$R_{out} \approx [g_{m2}r_{o1}r_{o2}A_1].$$

A. Amplifier Stability

The frequency analysis of the amplifiers are included. In order to achieve stability, they are compensated with 500fF capacitors. The amplifiers are tuned so that they provide approximately the same gain and both achieve slightly greater than 60 degrees of phase margin. The response operates very close to a critically damped system, resulting in small overshoot and settling time. The poles are determined from the phase plot at 10kHz and 100MHz.

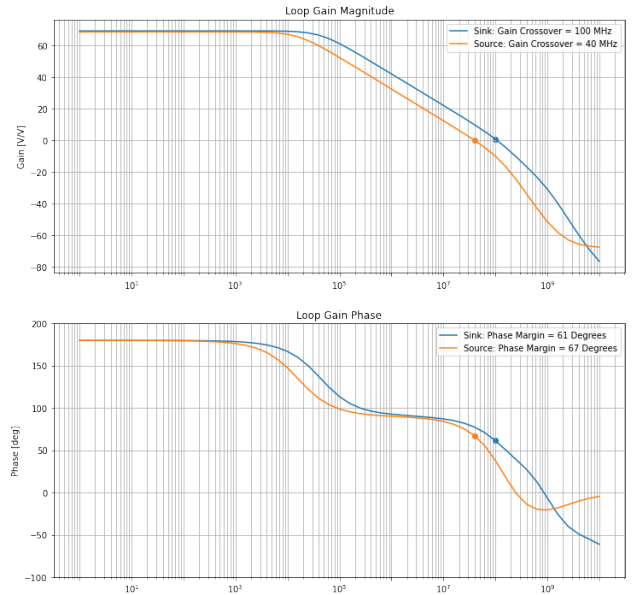


Fig. 2: Current Sink Driver Stability

B. PMOS Differential Pair Telescopic

The ideal gain for a telescopic differential pair is defined as

$$A_v = g_{m1}(g_{m2}r_{o4}r_{o5}||g_{m6}r_{o6}r_{o7}) = 4288.$$

The measured gain is 3810, which accounts for the losses due to the tail current source and non-ideality.

Name	Device	W	L	g_m	r_{out}
M0	nch	5.3u	933n	304.8u	83.08K
M2	nch	9.81u	786.4n	460.2u	94.52K
M4	pch	4u	935n	137.2u	502.2K
M5	pch	4u	930n	138.9u	779.2K
M6	pch	14u	880n	141.2u	509.9K
M7	pch	14u	880n	142.3u	939.1K
M8	nch	14u	880n	142.7u	939.0K
M9	nch	14u	880n	442.6u	900.8K
M10	nch	4u	880n	137.1u	499.5K
M11	nch	4u	880n	137.0u	499.6K
M20	nch	4u	600n	151.7u	161.1K

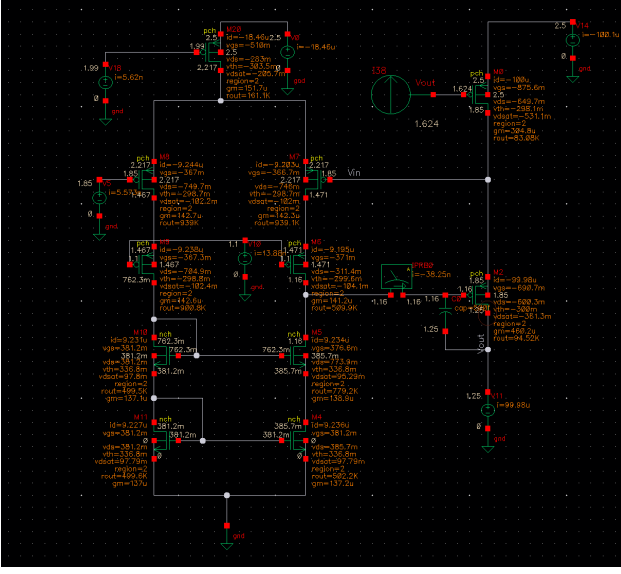


Fig. 3: Source Driver DC Operating Point

The source amplifier was originally designed to use the NMOS differential telescopic amplifier from the sink driver. The goal was to simplify and reuse as many components as possible. However, the biasing input voltage ultimately resulted in a design change. The NMOS differential input has to be large enough to keep the bottom cascode in saturation such that the input voltage is at least $V_{DD}/2 + V_{DSat,Cas}$. The telescopic amplifier also must support several V_{DSat} from $V_{in} - V_{gs}$. This bias requirement is very difficult to achieve. Thus, our driver design implements a PMOS differential telescopic amplifier which supports all the device requirements.

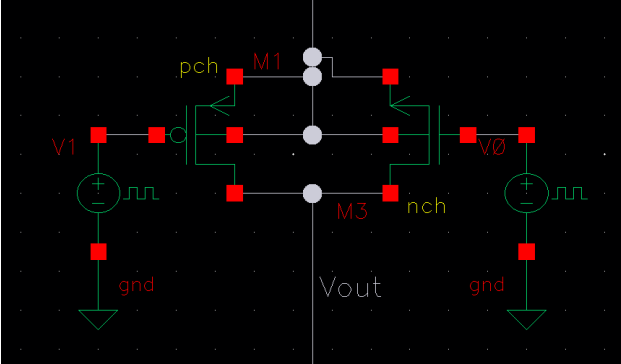


Fig. 4: Source Driver Switch

III. RESULTS

The total output resistance of the source driver is $8.28G\Omega$ with a current of $99.79\mu A$. This is very close to the updated sink output resistance of $8.32G\Omega$ with a current of $99.88\mu A$. Ideally, we want the two drivers to match as close as possible in current and resistance so that the electrode sees no difference between the charge taken and deposited. This solution prioritizes matching the source and sink drivers rather than achieving marginally improved gain and/or resistance in a single driver.

The electrode waveform of the full solution including physical switches is provided. The resulting wave forms show the precise work of our design and demonstrate very low variance between peaks. In the first plot, the voltage waveform reaches it's steady state after a single period and has a very predictable swing every following period. The second plot shows the simulated current pulses. We came close to reaching our $100\mu A$ target, however it was limited by the non-ideal switch we placed in there both allowing some current to pass when the switch was off and limiting the voltage at the cascode. Lastly, the integral of the current is shown to evaluate the amount of charge deposited and withdrawn from the electrode. The charge balance is calculated by taking the difference of two points that are one period apart. From this we determined that we had a very low charge discrepancy, this is also discussed in the conclusion.

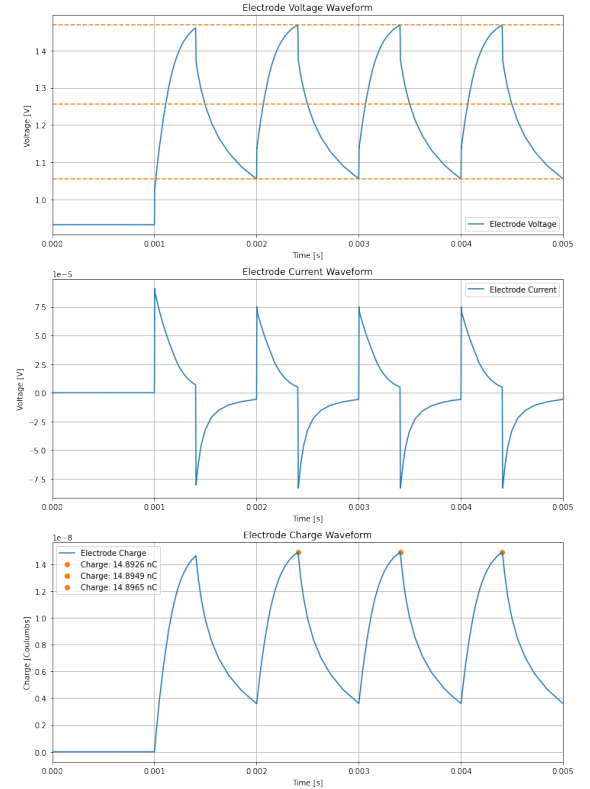


Fig. 5: Electrode Waveforms

Layout Cell / Type	Source Cell	Count	Nets	Instances	Ports
Incorrect Nets		4			
Discrepancy #1			EL_06 (+5)		
Discrepancy #2			OL_5S (-5)		
Discrepancy #3			OL_3S (-3)		
Discrepancy #4			OL_5S (-5)		
Incorrect Ports		2			
Discrepancy #5					
Discrepancy #6					
Incorrect Instances		5			
Discrepancy #7					
Discrepancy #8					
Discrepancy #9					
Discrepancy #10					

Cell SourceLayout (Incorrect Nets #1)	
LAYOUT NAME	SOURCE_NAME
Discrepancy #1 in SourceLayout	
Net 3	** no similar net **

Fig. 6: LVS: Incorrect Nets

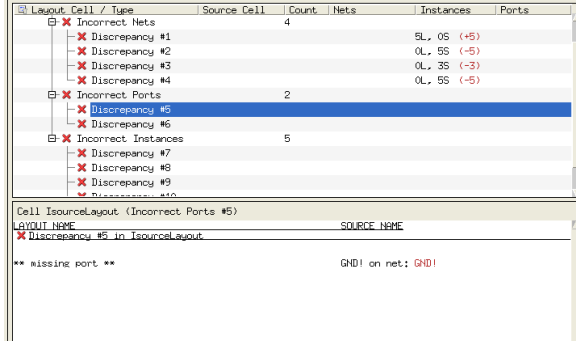


Fig. 7: LVS: Missing Ports

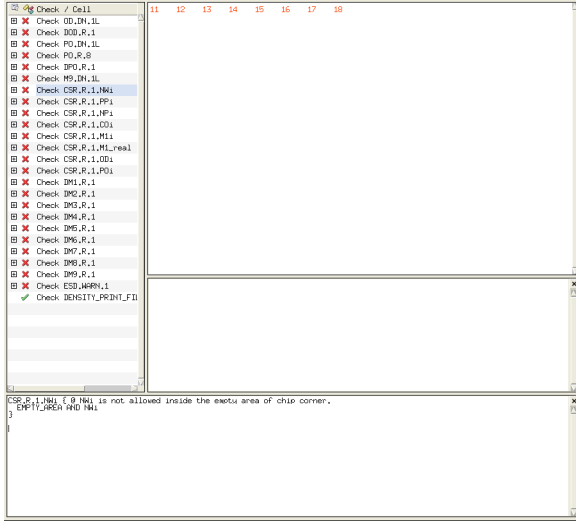


Fig. 8: DRC: Empty Area and NW

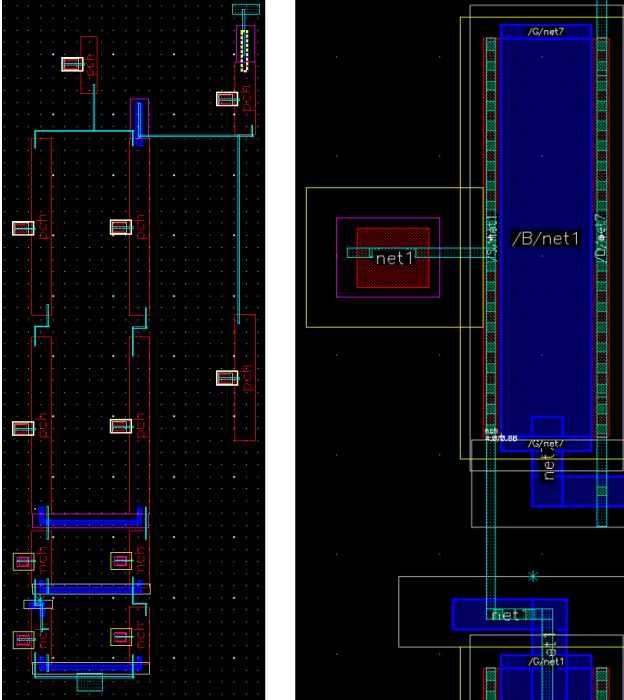


Fig. 9: Source Driver Layout

We were unable to achieve a perfect match from our schematic to the layout as seen in the LVS report. Most of the error messages were resolved, however, there are a few that couldn't be determined even with additional resources. Some of these errors are provided in V. *Additional Figures*.

For example, the LVS report lists that *net3* is not matched to our schematic, however, there is no *net3* on our schematic or layout. It also generated an error for not including our stability capacitor and stability test circuit, but it's unclear how to add those. Additionally, there was no GND! and PTAT IO pins despite there being both pins and labels for each.

The output from the DRC program is provided in Figure 8. The report shows many failed checks, with a lot of errors being related to the same thing. Similar to layout CAD project 3, we fixed all of the errors pertaining to sizing, n and p doped regions, oxide overlaps, contact sizes, etc. In the end, we were left with the following errors that we were unable to solve despite multiple attempts. Most remaining problems relate to chip space issues and missing layers that we did not recognize and are still unable to identify. We are unsure if they would create problems in fabrication or if they are harmless errors like we had at the end of CAD 3.

IV. CONCLUSION

The final result of our design is shown in the table below. Total power consumption was large because the design doesn't reuse currents and required a lot of power in the current sources. Total area used was also quite large because we were seeking to optimize the resistance of our source and sink by increasing R_{out} . We did this by dropping the current in the amplifiers as well as increasing L to reduce the λ term in the R_{out} equation. This resulted in the scaling of both the W and L of the transistors making our transistor area quite large.

The resulting charge mismatch was very close to zero and continued to decrease the longer the simulation ran. The charge difference between pulses was calculated as 1.6pC. The charge waveform shows approximately an 11nC swing on the electrode charge and equates to nearly a 0.015% error. The Voltage swing came out to be quite low. This was a result of using 1.85V and 0.6V as the two bias voltages of our op amps. In order for the devices to stay in saturation the voltage at the electrode needs to be larger than $0.6V + V_{DSat,Cas} + V_{DSat,Switch}$ and lower than $1.85V - V_{DSat,Cas} - V_{DSat,Switch}$ this calculates to our waveform swinging from about 1.05V to 1.45V.

In summary, the final design achieved very good matching between the sink and source currents and resulted in a very stable output on the electrode. However, this is not a very optimized design and could have a reduced power consumption and area used if more time went into its development.

If we had more time, we would have liked to place our focus on developing a more advanced switch for using with the electrode. Our switch created problems by reducing our voltage swing and inhibiting current to the electrode. With more time we could have created a more advanced switch that left less of an impact on our final current waveform.

Power Consumption	Transistor Areas	Charge Mismatch	Voltage Supply	Voltage Output Swing
0.75mW	$436\mu m^2$	$1.6pC$	2.5V	0.41V

V. ADDITIONAL FIGURES

```
DM1.R.1 { @ DM1 is a must. The DM1 CAD layer (TSMC default, 31:1 for DM1) must be different from the M1 CAD layer.
} CHIPx NOT INTERACT DUM1
```

Fig. 10: Error Message: DM1.R.1

```
PO.DN.1L { @ Min. POLY density across full chip >= 14%
  DENSITY ALL POLY CHIP < PO.DN.1L INSIDE OF LAYER CHIPx PRINT PO.DN.1L.density
  [ AREA(ALL_POLY)/AREA(CHIP) ]
}
```

Fig. 11: Error Message: P0.DN.1L

	W	L	Area				
Source Driver							
M0	5.30E-06	9.35E-07	4.96E-12		PMOS Cascode		
M2	9.81E-06	9.30E-07	9.12E-12		1.25V*99.79uA	0.0001247375	
M4	4.00E-06	8.80E-07	3.52E-12				
M5	4.00E-06	8.80E-07	3.52E-12				
M6	1.40E-05	8.80E-07	1.23E-11		PMOS Op Amp		
M7	1.40E-05	8.80E-07	1.23E-11		2.5V * 18.46uA	0.000046175	
M8	1.40E-05	8.80E-07	1.23E-11				
M9	1.40E-05	8.80E-07	1.23E-11				
M10	4.00E-06	8.80E-07	3.52E-12				
M11	4.00E-06	8.80E-07	3.52E-12				
M20	4.00E-06	6.00E-07	2.40E-12				
Source PTAT							
M0	6.00E-06	1.30E-06	7.80E-12		Source PTAT		
M1	6.00E-06	1.30E-06	7.80E-12		2.5V * 82.49uA	0.000206225	
M3	6.00E-06	1.30E-06	7.80E-12				
M21	6.00E-06	1.30E-06	7.80E-12				
R1		298 Ohms					
Q0	5.00E-06	5.00E-06	2.50E-11				
Q1 (n=2)	5.00E-06	5.00E-06	5.00E-11				
Sink Driver							
M4	1.20E-05	7.50E-07	9.00E-12		NMOS Op Amp		
M5	1.20E-05	7.50E-07	9.00E-12		2.5V * 35.23uA	0.000088075	
M6	9.00E-06	7.50E-07	6.75E-12				
M7	9.00E-06	7.50E-07	6.75E-12				
M8	9.00E-06	7.50E-07	6.75E-12				
M9	9.00E-06	7.50E-07	6.75E-12				
M10	1.20E-05	7.50E-07	9.00E-12				
M11	1.20E-05	7.50E-07	9.00E-12				
M18	2.00E-06	2.00E-07	4.00E-13		PMOS Cascode		
M19	1.58E-06	6.00E-07	9.45E-13		1.25V*99.88uA	0.00012485	
M20	2.00E-06	1.40E-06	2.80E-12				
Sink PTAT							
Q1	5.00E-06	5.00E-06	2.50E-11		Sink PTAT		
Q2 (n=2)	5.00E-06	5.00E-06	5.00E-11		2.5V * 63.4uA	0.0001585	
M0	2.00E-06	1.40E-06	2.80E-12				
M1	2.00E-06	1.40E-06	2.80E-12				
M2	2.00E-06	1.40E-06	2.80E-12				
M3	2.00E-06	1.40E-06	2.80E-12				
M4	2.00E-06	1.40E-06	2.80E-12				
R1		4.60E+04					
						Total Power Consumed (W)	
SUM			2.62E-10			0.0007485625	

Fig. 12: Transistor Summary