

Synergizing Hyper-Accelerated Power Optimization and Wavelength-Dependent QoT-Aware Cross-Layer Design in Next-Generation Multi-Band EONs

Farhad Arpanaei¹, Member, IEEE, Mahdi Ranjbar Zefreh², Yanchao Jiang³, Member, IEEE, Pierluigi Poggiolini⁴, Fellow, IEEE, Kimia Ghodsifar, Hamzeh Beyranvand⁵, Carlos Natalino⁶, Member, IEEE, Paolo Monti⁷, Senior Member, IEEE, Antonio Napoli⁸, José M. Rivas-Moscó, Óscar González de Dios, Juan Pedro Fernández-Palacios, Octavia A. Dobre⁹, Fellow, IEEE, José Alberto Hernández¹⁰, Member, IEEE, and David Larrabeiti¹¹

Abstract—The extension of elastic optical network (EON) technologies to multi-band transmission (MB-EON) promises enhanced spectral efficiency, greater throughput, and long-term cost benefits for telecom operators. However, designing such networks presents challenges, particularly in optimizing physical parameters like optical power and quality of transmission (QoT) across different frequency bands. This paper introduces a methodology for optimal span-by-span power allocation using two hyper-accelerated power optimization (HPO) modes: flat launch power (FLP) and flat received power (FRP). This methodology significantly accelerates network power optimization while ensuring service stability in scenarios such as changes in network parameters, QoT degradation due to aging, and network re-optimization or upgrading. Through a comprehensive comparison, we find that FRP notably improves signal flatness and GSNR/OSNR, particularly in the S-band, contributing to a network-wide throughput increase in the order of 12% to 75%.

Additionally, we demonstrate that HPO applied to global power optimization is simpler and more cost-effective than when applied to local methods for large-scale networks.

Index Terms—Multi-band, elastic optical networks (EONs), quality of transmission (QoT), power optimization, LOGON.

I. INTRODUCTION

THE multi-band (MB) technology is a cost-effective solution to address the growing demand for higher bandwidth in metro and core networks, which experience an annual traffic demand increase of more than 35%-40% [1], [2], [3]. However, the adoption of this technology is currently in the early stages, with only the L+C (LC)-band having been recently commercialized [4], [5]. In addition to the hardware requirements associated with implementing the LC-band and beyond, such as amplifiers and transceivers, the planning of MB optical networks require addressing the inter-channel stimulated Raman scattering (ISRS) effects. ISRS causes the power of high-frequency channels to deplete into the low-frequency channels. This phenomenon becomes particularly significant when the dense wavelength division multiplexing (DWDM) bandwidth is wider than 10 THz [6]. Network planning becomes even more complex in EONs when the choice of the modulation format for a lightpath varies based on the distance, number of spans, and the number of traversed reconfigurable optical add-drop multiplexer (ROADM) components. Several works in the literature have studied how to address the challenges of planning MB-EONs. One of the challenges is the power optimization and control of channels, where the literature has focused on various objective functions such as link capacity maximization [7], [8], or the flatness of the signal-to-the-noise ratio profile [9]. However, available solutions may not be rapid enough for the online provisioning in dynamic MB-EONs, and may require costly devices such as dynamic gain equalizers (DGEs) at every span. Moreover, various resource allocation algorithms have been proposed, but often do not take into account all the numerous physical layer effects in the fiber. Therefore, the planning of MB-EONs deserves more detailed analyses considering more complete physical layer modeling.

Received 4 April 2024; revised 17 September 2024; accepted 1 November 2024. Date of publication 19 February 2025; date of current version 14 May 2025. This work was supported in part by the Universidad Carlos III de Madrid (UC3M), Telefonica, and Infinera funded by the EU-funded ALLEGRO Project under Grant 101092766; in part by UC3M through Spanish-funded Fun4date-Redes Project under Grant PID2022-136684OB-C21; and in part by EU-funded FLEX-SCALE Project under Grant 101096909. The work of Farhad Arpanaei was supported by the CONEX-Plus Program funded by UC3M and European Union's Horizon 2020 Research and Innovation Program under the Marie Skłodowska-Curie under Grant 801538. The work of Octavia A. Dobre was supported in part by the Natural Sciences and Engineering Research Council of Canada (NSERC) through its Discovery Program. (Corresponding author: Farhad Arpanaei.)

Farhad Arpanaei, José Alberto Hernández, and David Larrabeiti are with the Department of Telematic Engineering, Universidad Carlos III de Madrid (UC3M), Leganés, 28911 Madrid, Spain (e-mail: farhad.arpanaei@uc3m.es).

Mahdi Ranjbar Zefreh is with Cisco Systems S.R.L., 20871 Vimercate, Italy. Yanchao Jiang and Pierluigi Poggiolini are with the Politecnico di Torino, 10129 Turin, Italy.

Kimia Ghodsifar was with the Department of Electrical Engineering, Amirkabir University of Technology (Tehran Polytechnic), Tehran 159163-4311, Iran. She is now with the University of Waterloo, Waterloo, ON N2L 3G1, Canada.

Hamzeh Beyranvand is with the Department of Electrical Engineering, Amirkabir University of Technology (Tehran Polytechnic), Tehran 159163-4311, Iran.

Carlos Natalino and Paolo Monti are with the Electrical Engineering Department, Chalmers University of Technology, 41296 Gothenburg, Sweden. Antonio Napoli is with Infinera, 81541 München, Germany.

José M. Rivas-Moscó, Óscar González de Dios, and Juan Pedro Fernández-Palacios are with Telefónica Global CTIO, 28050 Madrid, Spain.

Octavia A. Dobre is with the Faculty of Engineering and Applied Science, Memorial University, St. Johns, NL A1C 5S7, Canada.

Digital Object Identifier 10.1109/JSAC.2025.3543528

This work focuses on the performance analysis of MB-EONs under realistic network scenarios. We propose a new algorithm for power optimization that optimizes the per-span power with low complexity and fast solution time. We evaluate the proposed algorithm in a network-wide scenario by simulating the proposed algorithm using two resource assignment algorithms. The simulation scenario takes into account the numerous physical layer effects in the fiber relevant for MB-EONs. Therefore, the main contributions of this manuscript can be summarized as follows: (i) We propose hyper-accelerated power optimization approach for uniform and pre-tilt launch power profiles, termed flat launched power (FLP) and flat received power (FRP); (ii) We propose a wavelength-dependent QoT-aware modulation cardinality index selection and spectrum assignment based on a Flexponder; (iii) We conduct exhaustive simulations across various span lengths and network configurations to demonstrate the efficacy of the proposed HPO algorithm; (iv) We compare the performance of local optimization versus global optimization to assess the algorithm's effectiveness. Our research reveals that while FRP does not notably increase total capacity (showing an increase of less than 10 Tbps for an L+C+S (LCS)-band system spanning 100 km), its impact is negligible for systems operating in the C- and LC-band scenarios. However, in the LCS scenario, FRP brings notable improvements in flatness (the difference between maximum and minimum values) and the minimum value of the generalized signal-to-noise ratio (GSNR)/optical SNR (OSNR), especially in the S-band, achieving approximately 2/0 dB and 2.5/6 dB, respectively. In the network-wide analysis with several network topologies, the improvement in the minimum GSNR due to the FRP technique, synergizing with wavelength-dependent QoT-aware cross-layer design, results in a throughput increase ranging from approximately 12% to 75% (depending on the network scale) at a 1% bandwidth blocking rate. Lastly, we apply HPO to local and global power optimization methods in MB-EON, showing that, while both methods exhibit similar performance, the latter is simpler and more cost-effective for larger-scale networks due to not needing DGEs at each span. It should be noted that a preliminary version of the HPO method for the CL-band was presented in [10].

The rest of this paper is structured as follows: Sections II provide the background necessary for this work.. Section III provides a summary and analysis of the QoT estimator and physical layer modeling. Section IV describes the node and network architecture compatible with the proposed cross-layer design methodology. Section V introduces the power optimization algorithm proposed in this paper, describing the FLP and FRP modes. Section VI evaluates the performance of the proposed solution. Finally, Section VII presents the conclusions of this paper.

II. STATE-OF-THE-ART TECHNIQUES IN POWER OPTIMIZATION AND QoT-AWARE NETWORK PLANNING IN MB-EONS

The planning and service provisioning of MB-EONs has been studied over the past years covering four main areas: (i) migration scenarios from the C-band to beyond C-band, including C to LC / L+C+D (LCS) / LCS+E / LCS+E+O /

TABLE I
SUMMARY OF THE RELATED WORKS. $\alpha(f)$ IS
THE FIBER LOSS COEFFICIENT

Reference	QoT-Aware Cross-Layer Design of MB-EONs							
	ISRS effect on NLI (SPM+XPM)	ISRS effect on ASE	ISRS effect on $\alpha(f)$	Optimum flat received power	ASE-shaped Noise Filler	ML-based GN/EGN CFM [19], [22], [23]	Flexponder Grooming	Wavelength-Dependent
[11]	✓	✓	✓	×	✓	×	×	×
[20]	✓	×	×	×	×	×	×	×
[9]	✓	✓	✓	×	✓	×	×	×
[24]	×	✓	×	×	×	×	×	✓
[21]	✓	×	×	×	×	×	×	×
[25]	✓	✓	×	×	×	×	×	×
[26]	✓	×	×	×	×	×	×	×
This study	✓	✓	✓	✓	✓	✓	✓	✓

U+LCS+E+O transitions [1], [11], [12]; (ii) techno-economic studies [1], [3], [12]; (iii) power optimization and control strategies [7], [9], [13], [14], [15], [16], [17], [18], [19]; and (iv) routing, modulation format, band, and spectrum/wavelength assignment algorithms (RMBS(W)A) [11], [20], [21]. This paper focuses on the greenfield network planning for MB-EONs, and different migration strategies (e.g., day-one and pay-as-you-grow) or techno-economic studies are out of its scope. Therefore, in the following, we discuss state-of-the-art power optimization and RMBS(W)A algorithms. We provide an overview of the key related works in Table I.

Regarding power optimization, previous works have considered various objective functions such as link capacity (i.e., achievable information rate) maximization [7], [14], [19], minimum GSNR maximization [13], or flatness of the GSNR profile in each band or across all bands [9], [15], [27]. However, solving the power optimization problem while considering the ISRS effects is challenging due to its NP-hard and non-convex nature [7], [16]. To address this challenge, various brute-force heuristic and meta-heuristic algorithms have been proposed, including genetic algorithm [15], particle swarm optimization [7], [17], and greedy search [9], [18]. Additionally, while some authors have tackled the problem on a channel-by-channel basis [7], [16], others have adopted a span-based approach by considering auxiliary parameters. For instance, in [9] and [18], the authors proposed using two auxiliary parameters for each band: fixed tilt (slope) and offset, known as the (*tilt*, *offset*) approach. Moreover, the authors in [8] recently proposed a heuristic power optimization algorithm named ASE-NL for MB-EONs based on the LOGON strategy (local optimization-global optimization, where “N” represents Nyquist [28]). This algorithm iteratively adjusts the mean and tilt of the amplifier gain to set the ASE noise power to twice the Kerr Nonlinear (NL) noise power. Three approaches were studied, and the results showed that the

capacity maximization strategy outperformed both the in-band and intra-band GSNR flatness approaches in terms of served capacity. This approach is similar to the exhaustive search method described in [9] for finding the mean and tilt of the gain profile. Additionally, in [19], four parameters require tuning, i.e., offset, slope, parabolic, and cubic constants. Although these span-based approaches offer faster solutions compared to the channel-by-channel ones, they may not be rapid enough for online provisioning in dynamic planning scenarios.

All these proposed approaches involve analyzing an extensive search space [8], [9], [18], [19]. This is evidenced by the solution time in the order of several minutes [9] or even hours [7]. Furthermore, as demonstrated in [29], for C-band WDM systems, considering flat received power at the end of the span as an objective function results in higher link capacity compared to using flat GSNR as the objective function. Additionally, the authors in [13] and [15] have shown that minimum GSNR maximization or optimizing GSNR flatness as an objective function does not maximize the system capacity. The uniformity of the OSNR, rather than the GSNR, becomes particularly significant, especially when different channels or lightpaths exhibit varying GSNR values due to the disparate routes they follow [30]. Therefore, we opt to focus on maintaining a uniform power level at the end of each span, instead of using flat GSNR as the objective function, aiming at the system capacity maximization.

Regarding RMBS(W)A algorithms, aspects related to traffic assumptions, fixed- vs. flexi-grid, and traffic grooming have been the topic of several research efforts. Various approaches to static [20], semi-static [24], and dynamic [11] RMBS(W)A have been explored. In static planning, the traffic matrix is known in advance, and services have infinite holding time. Semi-static planning involves unknown traffic matrices, but assumes infinite service holding times. Dynamic planning deals with unknown traffic matrices and holding times. The routing in optical network planning typically relies on the k -shortest path first (K-SPF) algorithm. This involves selecting the shortest path (based on distance, number of optical hops, or multiplexing sections) with sufficient available spectrum resources as the primary choice. However, some studies have explored alternative criteria such as maximizing GSNR [9], [24] or minimizing the cost of the load balancing factor [31] when selecting paths. Additionally, distance-adaptive network planning [20], [21], [26] has been explored, with some studies considering worst-case channel scenarios [9], [11] for modulation cardinality index selection, determining the line card interfaces' (LCIs) bit rate capability. In this work, our analysis is based on semi-static network planning which is considered the most practical case in backbone networks [32].

While recent works have addressed both fixed-grid [9] and flexi-grid [20] MB-EONs, the latter poses practical challenges due to ISRS effects. Despite efforts to apply flexi-grid EONs, developing a closed formula to estimate power profiles, even for LC-band scenarios, remains unfeasible [23]. Some authors have focused on QoT-aware network planning [20], [24] but have overlooked the amplified spontaneous emission

(ASE)-shaped noise filler for idle channels [5], resulting in unaddressed power profile changes and QoT degradation in established lightpaths.

Recent works have also discussed how optical layer grooming can be achieved, with transponders and Flexponders figuring as the two main alternatives. In transponder grooming [9], [24], each client card interface is connected to an LCI, with IP flows groomed from the client card to the corresponding LCI. Modern modems operate based on the Flexponder concept, allowing low-bit-rate IP flows between a source-destination to be groomed at any LCI with sufficient capacity and the same source-destination. As the GSNR of each channel varies, the modulation cardinality of each LCI differs based on the frequency work point. Wavelength-dependent QoT considerations, as discussed in this paper, can reduce blocking probability and result in cost savings through optimized LCI usage. Therefore, this manuscript considers real-world MB-EONs in which the bit rate variable LCIs are achieved by adjusting the modulation cardinality. Therefore, we assume to transmit signals with quadrature amplitude modulation (QAM), where the modulation format of the LCIs can be adjusted based on the QoT for each connection (or lightpath).

III. QoT ESTIMATION TOOL AND PHYSICAL LAYER MODELING

This section describes the physical layer modeling and QoT estimation, followed by an examination of our methodology. In this paper, we specifically address the GSNR when referring to the QoT, accounting for linear and non-linear noise components.

A. End-to-End QoT Estimator

The Gaussian-noise (GN) model [28] is utilized to examine the effects of both linear factors, such as loss and chromatic dispersion, and non-linear interference (NLI) effects such as self-phase modulation (SPM), cross-phase modulation (XPM), multi-channel interference (MCI), and ISRS, on the optical signals' amplitude and/or phase modulation as they propagate through an optical fiber medium. Since we have considered the standard single-mode fiber (SSMF) and we are not working in zero or very low fiber dispersion regimes, the MCI is negligible [23]. Consequently, the computation of GSNR (denoted as Γ) for a specific channel i within span s on link l is achieved using (1) and (2):

$$\Gamma^{l,s,i} \cong \frac{P}{P_{\text{ASE}}^{l,s,i} + P_{\text{NLI}}^{l,s,i}}, \quad (1)$$

$$P = \begin{cases} P^{l,s+1,i}(z=0) & ; \quad \text{if } s < N_s^l, \\ P^{l+1,1,i}(z=0) & ; \quad \text{if } s = N_s^l, l < N_L, \\ P^{l,s,i}(z=0) & ; \quad \text{if } s = N_s^{N_L}, \end{cases} \quad (2)$$

where N_s^l represents the number of spans in link l , while N_L denotes the link number of the corresponding lightpath (LP). Utilizing the incoherent GN model for long enough spans, the value of the overall GSNR for a LP on channel i can be

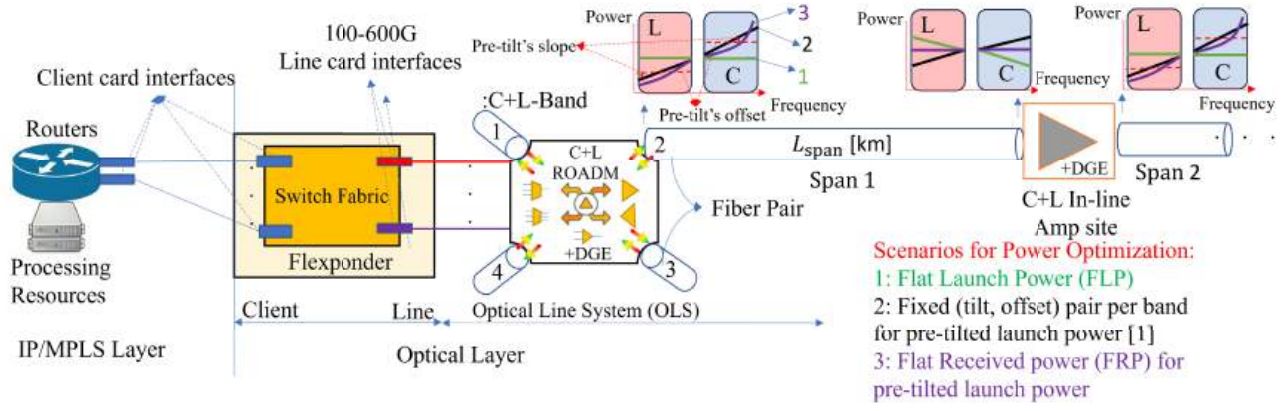


Fig. 1. A cross-layer architecture is proposed for MB-EONs, focusing on illustrating C+L-band systems for simplicity.

obtained from (3):

$$\Gamma_{LP}^i|_{dB} = 10 \log_{10} \left[\left(\sum_{l=1}^{N_L} \sum_{s=1}^{N_s^l} \frac{1}{\Gamma_{l,s,i}^{l,s,i}} + \Pi_{TRx}^{-1} \right)^{-1} \right] - \Pi_{Pen_{fil}}|_{dB} - \Pi_{Pen_{age}}|_{dB}, \quad (3)$$

where various parameters contribute, such as the power evolution profile (PEP) of each span ($P^{l,s,i}(z), 0 \leq z \leq L_s^l$), the length of span s in link l (L_s^l), the noise power caused by the optical amplifier ($P_{ASE}^{l,s,i}$ calculated from (4)), and the noise power stemming from NLI ($P_{NLI}^{l,s,i}$), including SPM, XPM, and ISRS. The details regarding computing ($P_{NLI}^{l,s,i}$) is discussed in the section III-B.

$$P_{ASE}^{l,s,i} = n_F h f_i (G^{l,s,i} - 1) R_{sym,i}, \quad (4)$$

In (4), n_F , h , f_i , $G^{l,s,i}$, and $R_{sym,i}$ are the noise figure of doped fiber amplifier (DFA), Plank's coefficient, channel frequency, the gain of DFA, and channel symbol rate, respectively. Additionally, Π_{TRx} , $\Pi_{Pen_{fil}}$, and $\Pi_{Pen_{age}}$ represent the transceiver SNR, SNR penalty due to wavelength selective switches (WSSs) filtering, and SNR margin due to aging, respectively [17], [33], [34]. Furthermore, the channel bandwidth ($B_{ch,i}$) and bit rate of each channel with modulation cardinality m ($R_{ch,(i,m)}$) are calculated from $B_{ch,i} = \left\lceil \frac{R_{sym,i}(1+\rho_i)}{B_{Base}} \right\rceil B_{Base}$, and $R_{ch,(i,m)} = m R_{sym,i}(1+\rho_i)(1-\theta)$, respectively. Here, parameters like the symbol rate of the channel ($R_{s,i}$), the roll-off factor (ρ_i), the forward error correction (FEC) overhead (θ), and the bandwidth of a base frequency slot (B_{Base}) are involved. Moreover, the GSNR threshold for each modulation format level depends on the pre-FEC bit error rate (BER) and can be determined using (8) in [12]. It is assumed that the booster gain at the add and pass-through directions are $G^{l,s,i} = 20$ dB, and the pre-amplifier can completely compensate for the fiber loss of the link and the QoT degradation caused by ISRS. Thus, for the pre-amplifiers and in-line amplifiers, the following expressions can be written:

$$G^{l,s,i} = P / P^{l,s,i}(z = L_s^l), \quad (5)$$

where P (see (2)) and $P^{l,s,i}(z = L_s^l)$ are the powers of channel i just after and before the corresponding amplifier, respectively. For instance, consider the flat launch power

(FLP) mode in span 1, as illustrated in Fig. 1. In other words, based on (4) and (5), the $P_{ASE}^{l,s,i}$ depends on the PEP. As shown later in (10), the PEP is influenced by ISRS, where higher-frequency channels transfer power to lower-frequency channels. Therefore, the ASE noise is dependent on ISRS through the amplifier's gain profile. In this regard, in-line amplifier (ILA) sites are equipped with DGE to balance the power/gain profile based on the received power at the ILA input and the launch power profile at its output. The DGE could be implemented using wavelength-selective switches (WSS) and variable optical attenuators, which adaptively adjust the power of each wavelength based on the input and output power, as shown in Fig. 1.

Finally, to create a practical model for the optical line system penalties, we applied a range of factors: randomly assigning connector losses between 0.2 to 0.5 dB, factoring in ROADMs' polarization dependent loss at 0.5 dB per node along the lightpath, and randomly accounting for splice losses in the range of 0.01 to 0.06 dB/km. The average length of the fusion splicing sections is considered 2 km [35].

B. Physical Layer Model

Acquiring precise values for all parameters in GSNR calculation is often complex and sometimes unfeasible. Nevertheless, through the application of state-of-the-art telemetry and AI-based approaches [36], [37], we can characterize physical layer parameters such as the noise figure of the amplifiers, ROADMs' filtering penalty, and SNR_{TRx} . Assuming we possess acceptable knowledge of these physical layer parameters, the most challenging aspect of GSNR estimation for MB-EONs lies in estimating $P_{NLI}^{l,s,i}$ and $P_{ASE}^{l,s,i}$, with the ISRS effects playing a predominant role. However, while the NLI models in the time-frequency domain offer the highest accuracy, they rely on solving complex integrals and are unsuitable for online or offline network planning tools [28]. The computational time needed by models like the split-step Fourier method, integral-based GN model, and enhanced GN model (EGN) is excessively high [38]. Furthermore, they are too complex to adequately account for the add/drop effect modeling in network-wide level studies. Consequently, over the past several years, several closed-form transmission models (CFMs) (e.g., [6]) and semi-CFMs (e.g., [23], [39]) have

been developed to estimate NLI. CFMs provide closed-form formulas for PEP and NLI but rely on specific assumptions for each model, e.g., triangular shape for Raman gain profile [6]. If the system model does not align with these assumptions, the model's accuracy diminishes. Semi-CFM, on the other hand, calculate PEP and loss coefficients using fitting approaches, allowing for flexibility in ignoring certain assumptions. Additionally, the generalized GN model (GGN) is a well-known GN integral-based QoT estimator widely used in DWDM systems, offering acceptable accuracy but lacking modulation format correction terms crucial for MB-EONs [40]. Four fast CFMs have recently surfaced in the literature, as discussed in [6], [41], [42], and [43]. The authors of [42] compared the models proposed in [6] and [41] with the GGN model [40], which is utilized in GNPY [44]. They found that the model presented in [6] demonstrates the highest accuracy for LCS1-band scenarios, particularly when additional correction forms are incorporated. However, their investigation primarily focused on Gaussian-shaped signals. Conversely, the authors of [43] introduced a CFM that considers Raman windowing sweeping across the frequency axis to enhance the accuracy of the model proposed in [6], specifically for LC-band scenarios.

Two semi-CFM introduced in [23] and [39] offer adequate accuracy for EONs beyond 15 THz, i.e., the C+L+S1-band. In this paper, we employ the model in [19] and [23] that uses the most advanced techniques, which is a machine learning (ML)-based GN/EGN model that has been validated through both the split-step Fourier method and experimental testing [45]. In addition, it incorporates essential features such as dispersion and modulation format correction terms, striking a fine balance between accuracy and speed. Therefore, $P_{\text{NLI}}^{l,s,i}$ is estimated from (6), as shown at the bottom of the next page.

To estimate the $\Gamma^{l,s,i}$ of each span, we follow the methodologies outlined in [19], utilizing (1)–(6). The process involves the following steps:

Step 1: Numerically calculating the PEP by solving a system of coupled differential equations, i.e., (10) detailed in Section V. This necessitates the launch power profile, fiber loss coefficient profile, and the ISRS gain profile function. Notably, the ISRS gain is contingent upon factors such as the pump channel frequency, the discrepancy between pump and signal channels, and fiber physical parameters like effective area, diffraction coefficient, and numerical aperture value.

Step 2: Estimating auxiliary loss coefficients profiles, i.e., $\alpha_0(f)$, $\alpha_1(f)$, and $\sigma(f)$ by fitting the power evolution profile obtained from step 1 and approximately closed-form formula, (13) in [23]. The inspired actual frequency-dependent fiber loss can be loosely modeled based on (7).

$$\alpha(z, f_i) = \alpha_0(f_i) + \alpha_1(f_i) \exp\{-\sigma(f_i)z\}, \quad (7)$$

where z is the signal propagation distance, and the index i to denote the channel's frequency f_i . Indeed, the interpretation of (7) suggests that the observed loss coefficient in MB systems differs from the loss coefficient utilized in C-band systems. In this context, $\alpha_0(f_i)$ represents the fiber loss in the absence of ISRS, while $\alpha_1(f_i)$ quantifies the loss alteration attributable to ISRS at the onset of the span. Additionally, $\sigma(f_i)$ characterizes the rate at which ISRS diminishes along

the span with the decreasing optical power. Once these parameters are assigned, the NLI calculation becomes closed-form. However, assigning auxiliary loss coefficient profiles is not closed-form, as doing it in full closed-form would introduce excessive errors. This step is the only non-closed-form, being a semi-CFM QoT estimation approach. Equations (30.1) and (30.2) in [23] offer a closed-form best-fit for $\alpha_1(f_i)$ and $\alpha_0(f_i)$ given $\sigma(f_i)$. Finally, optimizing numerically over $\sigma(f_i)$ gives the overall best-fit for $\alpha_1(f_i)$, $\alpha_0(f_i)$, and $\sigma(f_i)$. For illustration, Fig. 2 presents the observed loss for a span length of 70 km in a fully loaded link with a flat launch power of 0 dBm. The results are obtained using the values outlined in Section VI for all the necessary parameters. As shown, the observed loss curve differs from the expected loss curves due to ISRS effects across various scenarios of the MB-EONs. Additionally, the results indicate that these differences become more pronounced with each additional band.

Step 3: Calculating $G^{l,s,i} = P/P_{\text{ASE}}^{l,s,i}(z = L_s^{l,s})$ to derive $P_{\text{ASE}}^{l,s,i}$.

Step 4: Computing the parameter M (please see (6)).

Step 5: Determining the effective dispersion profile (please see (6)). Here, f_0 denotes the frequency reference, which is associated with the wavelength 1550 nm, where β_2 , β_3 , and β_4 are measured (please see (6)).

Step 6: Establishing the frequency-dependent non-linearity coefficient ($\gamma_{i,j}$), where n_2 is the nonlinear (Kerr) refractive index and A_{eff} is the effective area (please see (6)).

Step 7: Finally, computing $P_{\text{NLI}}^{l,s,i}$ from (6), where $\psi_{i,j,p,k}$ is calculated from (8), $\delta_{i,j}$ is 1 if $i = j$ and 0 otherwise, and N_{ch} is the number of WDM channels. Finally, ρ_j is the machine-learning-based correction term (see [19] for details).

$$\psi_{i,j,p,k} = \text{asinh}\left[\frac{\pi^2 \bar{\beta}_2(f_j) R_{s,i}(f_j - f_i + (-1)^p R_{s,j}/2)}{2\alpha_0(f_j) + k\alpha(f_j)}\right] \quad (8)$$

Therefore, by substituting the values of $P_{\text{NLI}}^{l,s,i}$ and $P_{\text{ASE}}^{l,s,i}$ for each span in a LP, the total end-to-end GSNR can be calculated using (3). Therefore, with this modeling, we ensure that the effects of ISRS on ASE, NLI, and the loss coefficient, as represented in (4), (6), and (7), are properly accounted for.

IV. NODE ARCHITECTURES, AND TRAFFIC GROOMING

In this section, we outline the nodal and network architecture for the next-generation MB-EONs, where the optimal power of each span can be swiftly adjusted based on physical layer variations throughout the network's lifecycle [46].

A. Assumptions for Node Architecture

Each node is comprised of two layers as illustrated in Fig. 1: the IP/MPLS layer, housing routers, switches, and processing resources, and the optical layer, consisting of electrical-optical equipment such as Flexponders and ROADMs. Flexponders include client grey card interfaces, switch fabrics (optical transport network, i.e., ITU-T G.709 or a Muxponder), and colored line card interfaces (LCIs). Fig. 3 depicts LCIs with flexible modulation formats and bit rates. Leveraging state-of-the-art technologies like probabilistic constellation shaping, super-fast digital signal processing ASIC, and soft decision

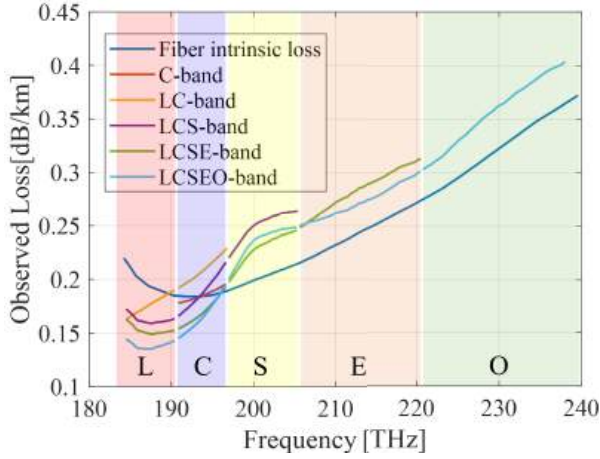


Fig. 2. ISRS effect on the fiber intrinsic loss for different multi-band systems. Span length = 70 km, launch power = 0 dBm, Fiber type: standard single mode fiber zero-peak water.

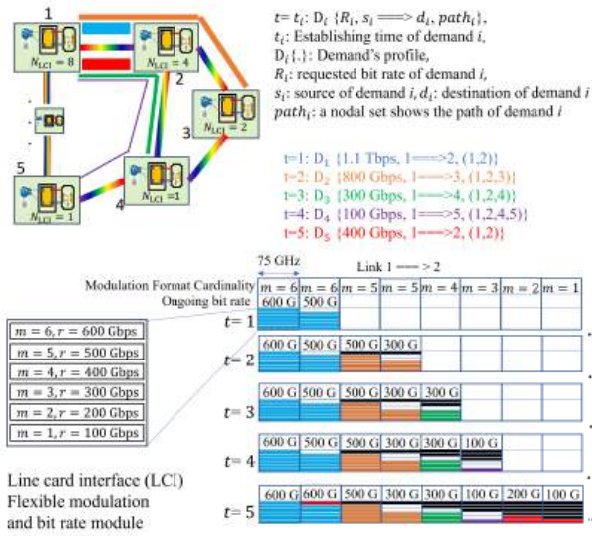


Fig. 3. Illustrative example for Flexpounder grooming based on the wavelength-dependent QoT-aware cross-layer design.

(SD)-FEC, LCIs can operate within a range of 100 Gbps to 1.6 Tbps over varying distances, with modulation format and FEC adjustments. For the sake of simplicity, we have considered LCIs ranging from 100 Gbps to 600 Gbps. Consequently, the GSNR gauge profile can reflect real-time QoT, and the bit rate can adapt according to the modulation format

of the LCIs. Hence, the software-defined networking (SDN) controller can dynamically adjust traffic grooming to allocate traffic to feasible LCIs. Client-side traffic from the IP/MPLS layer can be groomed electronically within the Flexponders and then forwarded to the LCIs (see Fig. 1). The architecture features colorless-directionless, and contentionless ROADMs-on-blade [12], which include boosters, pre-amplifiers, WSSs, and DGEs connected to fiber pairs. Each link (connecting two nodes) is divided into several spans (connecting cascaded in-line amplifier (ILA) sites), with the ILA site also incorporating DGEs to adjust launch power. It is worth noting that we assume the ILA site is equipped with gain and power controllers. Additionally, optical amplifiers within the ROADMs and ILAs for each band vary, requiring a multiplexer/demultiplexer before and after them.

B. Traffic Grooming

The network is assumed to be managed by a multi-layer SDN orchestrator capable of controlling both the optical and IP/MPLS layers. Consequently, when new demands arise, or the QoT of established LPs deteriorates due to hardware or software failures, a QoT-aware service provisioning procedure is initiated by the orchestrator and the relevant SDN agent controller in each layer. As depicted on the top of Fig. 3, we consider a network scenario highlighting five nodes and demands. Let us imagine that at $t = 1$, the links between nodes 1 and 2 ($1 \leftrightarrow 2$), ($2 \leftrightarrow 3$ and 4), and ($4 \leftrightarrow 5$) are idle. Each demand is characterized by a tuple $D_i = \{R_i, s_i \leftrightarrow d_i, path_i\}$ as shown on the top of Fig. 3. As mentioned in the previous section, LCIs can adaptively operate within a flexible range of modulation formats and bit rates, such as 100-600 Gbps corresponding to modulation cardinality $m = \{1, 2, 3, 4, 5, 6\}$. Moreover, based on [47], we assume that the idle channels are occupied by ASE-shaped noise to ensure network consistency. Therefore, whenever malfunctions leading to QoT degradation of LPs occur in the passive or active equipment of the optical layer, the proposed QoT-aware service provisioning procedure can be executed to optimize the network performance. As illustrated at the bottom of Fig. 3, the first two channels of link $1 \leftrightarrow 2$ are occupied by two LCIs belonging to an LP with a capacity of 1.1 Tbps and $path_i = 1 \leftrightarrow 2$. For D_i , based on the QoT estimator tool described in Section. III, both allocated LCIs operate with $m = 6$ but at different bit rates, i.e., 600 Gbps and 500 Gbps.

$$P_{NLI}^{l,s,i} = \frac{16}{27} P_{tx}^{s+1,i} \sum_{\substack{1 \leq j \leq N_{ch}, \\ 0 \leq p \leq 1, \\ 0 \leq k \leq M, \\ 0 \leq q \leq M}} \frac{\rho_j^2 (\gamma_{i,j})^2 (P_{tx}^{s+1,j})^2 (2 - \delta_{i,j}) (-1)^p e^{-4\alpha_1(f_j)/\sigma(f_j)} \left(\frac{2\alpha_1(f_j)}{\sigma(f_j)} \right)^{k+q}}{2\pi (R_{s,j})^2 k! q! (4\alpha_0(f_j) + (k+q)\sigma(f_j) \bar{\beta}_2(f_j))} \psi_{i,j,p,k},$$

$$\gamma_{i,j} = \frac{2\pi f_i}{c} \frac{2n_2}{A_{eff}(f_i) + A_{eff}(f_j)},$$

and,

$$\bar{\beta}_2(f_j) = \beta_2 + \pi\beta_3(f_i + f_j - 2f_0) + \frac{2\pi^2}{3} \times \beta_4[(f_i - f_0)^2 + (f_i - f_0)(f_j - f_0) + (f_j - f_0)^2],$$

$$M = \text{MAX}[10 \times \lceil 2\alpha_1(f_i)/\sigma(f_i) \rceil + 1].$$

(6)

This implies that the second LCI has 100 Gbps spare capacity for grooming upcoming demands with the same source and destination. Similar procedures are followed for the third and fourth demands established at $t = 3$ and 4. At $t = 5$, the traffic grooming of D_5 and D_1 occurs, and instead of using an additional LCI, we establish it only with two additional LCIs operating in channels 7 and 8. Therefore, we require 8, 4, 2, 1, and 1 LCIs in nodes 1, 2, 3, 4, and 5, respectively.

V. PROPOSED HYPER-ACCELERATED POWER OPTIMIZATION (HPO) ALGORITHM

According to [28], a sub-optimal power configuration for a Nyquist-WDM optical network can be achieved by determining the optimal power allocation for each span, a process referred to as LOGON. Specifically, this applies to an optical network utilizing Nyquist WDM channels with homogeneous spans, i.e., having identical physical layer characteristics such as length, noise figure, non-linearity, loss, dispersion coefficients, and fully loaded link state—the optimal flat launch power for each span can be computed based on (83) in [28]. It is important to note that these parameters are assumed to be frequency-independent. However, if these assumptions are violated, such as in multi-band systems where ISRS effects are considered and physical layer parameters become frequency-dependent, (82) in [28] cannot be directly utilized. Consequently, a closed-form solution for this optimization problem is not available. Hence, we propose a heuristic algorithm to determine the optimal flat launch/receive power per span. Although this approach may not guarantee optimality, it leverages the principles of LOGON to obtain a sub-optimal power configuration for the network. To do so, we aim at maximizing the total capacity (TC) [1] of each span while respecting the maximum launch power P_{\max} :

$$\begin{aligned} \text{MAX } TC^{l,s} &= 2 \sum_{\forall i \in \mathcal{C}} R_s^{l,s,i} \log_2(1 + \Gamma^{l,s,i}) \\ \text{s.t. } \mathbf{C1} : P^{l,s,i} &\leq P_{\max}, \forall i \in \mathcal{C}. \end{aligned} \quad (9)$$

For the sake of simplicity, we assumed that the input constellation has a Gaussian distribution in the calculation of TC [17], [48]. \mathcal{C} , \mathcal{S} , and \mathcal{L} represent the sets of channels, spans, and links, respectively. We assess two HPO modes: flat launch power (FLP) and flat received power (FRP). To accomplish this, we must calculate the PEP. In an MB-EON with $|\mathcal{C}|$ channels having center frequencies $f_1 < f_2 < \dots < f_{|\mathcal{C}|}$, the evolution of power over distance for each channel (or PEP) is governed by a system of coupled differential equations [23]:

$$\begin{aligned} &\frac{\partial P_{\text{tx}}^{l,s,i}(z)}{\partial z} \\ &= \kappa P_{\text{tx}}^{l,s,i}(z) \left[\sum_{\forall j \in \mathcal{C}} \zeta \left(\frac{f_i}{f_j} \right) \right. \\ &\quad \left. \times C_r(f_j, f_j - f_i) P(f_j, z) - \alpha(f_i) \right], \forall i \in \mathcal{C}, \end{aligned} \quad (10)$$

where z is the signal propagation distance, $\alpha(f_i)$ is the fiber attenuation at frequency f_i , $P_{\text{tx}}^{l,s,i}(z)$ is the power of the i^{th} channel at distance z , and κ is set to +1 for a signal propagating along the $+z$ direction (forward propagating),

Algorithm 1 HPO

Input: Span physical layer parameters, e.g., length, loss, dispersion, non-linearity coefficients, etc., and initial values such as P_{start} , P_{end} , P_{\max}

Output: Optimum TC, Launched and Received PEPs ($PEP_{L/R}$) and the Corresponding GSNR Profiles (Γ)

```

1:  $Max\_TC \leftarrow 0$ 
2: for  $P^i \in (P_{\text{start}} : 0.1 : P_{\text{end}})$  do
3:   Calculate  $TC(P^i)$  from (9)
4:   if  $\text{MAX} \{PEP\} > P_{\max}$  then
5:     break
6:   end if
7:   if  $TC(P^i) > Max\_TC$  then
8:      $Max\_TC \leftarrow TC(P^i)$ ,  $PEP_{L/R}^* \leftarrow PEP_{L/R}$ ,
        $\Gamma^* \leftarrow \Gamma$ , {L: Launch, R: Receive}
9:   else
10:    break
11:   end if
12: end for
13: return  $Max\_TC$ ,  $PEP_{L/R}^*$ ,  $\Gamma^*$ .
```

while $\kappa = -1$ for signals propagating in the $-z$ direction (backward propagating). $\zeta(x)$ returns x for $x > 1$, 0 for $x = 0$, and 1 for $x < 1$. C_r exhibits odd symmetry with respect to the frequency difference $\Delta f = f_j - f_i$. This variable characterizes the gain profile of the Raman effect within the fiber. It is contingent on the fiber's physical attributes, such as the Raman gain coefficient and the effective area of the fiber. In FLP mode, we set $\kappa = 1$ and restrict the range of acceptable launch power values to ensure a practical amplifier gain and total output power while managing nonlinear Kerr effects like SPM and XPM. A viable approach to counteract the ISRS effect is to incorporate a tilt in the output spectrum of the optical amplifiers in use, i.e., FRP mode. This tilt ensures a nearly uniform input spectrum into the subsequent optical amplifier, thus maintaining a consistent OSNR after each span and at the receivers. To achieve this, we set $\kappa = -1$ and again restrict the range of acceptable launch power values to ensure a practical amplifier gain and total output power while managing nonlinear Kerr effects. Our objective is to determine the highest possible span capacity under these conditions.

Algorithm 1 outlines the proposed HPO algorithm, which comprises the FLP and FRP modes. The same algorithm is defined for both FLP and FRP HPO modes. The only difference is in the flatness assumption of the power profile: in FLP, the transmitted power profile is assumed to be flat, while in FRP, the received power profile is assumed to be flat. In FLP mode, we set $P_{\text{start}} = P_{\text{LOGO}}$ and $P_{\text{end}} = P_{\text{LOGO}} + 3$, where P_{LOGO} can be determined using (83) in [28]. In FRP mode, we initiate our search with a starting channel power after propagation over a span of length L_{span} , calculated as $P_{\text{start}} = P_{\text{FLP,Opt}} - \alpha_{\max} L_{\text{span}}$, where $P_{\text{FLP,Opt}}$ represents the optimal FLP and α_{\max} is the maximum attenuation across all channel frequencies. Additionally, $P_{\text{end}} = 0$.

Alg. 1 starts by establishing a variable that tracks the highest achieved TC (line 1). Then, the algorithm iterates over each possible maximum launch power P^i (line 2). Following the

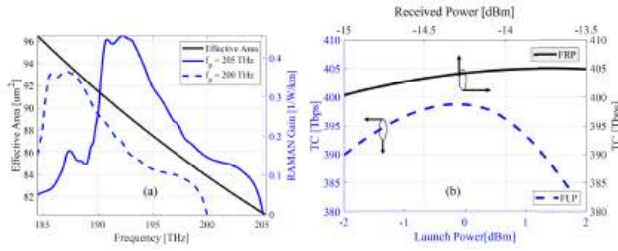


Fig. 4. (a) Effective area and Raman gain profile for two channels at 205 THz and 200 THz, (b) The hyper-accelerated power optimization algorithms, comparing flat launch power (FLP) with flat receive power (FRP), are evaluated for LCS-band scenario. The span length is set to $L_s = 70$ km.

launch power ranges defined in the previous paragraph, P^i increases in steps of 0.1. Then, the algorithm computes the TC achieved by P^i (line 3). If the PEP achieved by P^i violates the P_{max} constraint, P^i is not considered (lines 4-6). If the TC is increasing, the current metrics are saved as the best ones (lines 7-8). Once the algorithm finds one P^i that does not increase TC, it stops the iterations (lines 9-11), and returns the solution (line 13).

VI. SIMULATION RESULTS AND DISCUSSION

In this section, we compare FLP HPO against FRP HPO at both the span level and network-wide level. In the span level analysis, various multi-band scenarios, including C-, CL-, and LCS-band, are considered for spans ranging from 50 km to 100 km. The statistical values of the GSNR and OSNR profiles are reported to illustrate the performance of both FLP and FRP in the span-level study. Next, we move on to the network-wide analysis, where we evaluate the performance across three different-sized networks: small-scale (Spain), medium-scale (Japan), and large-scale (United States of America) backbone networks. The parameters assessed include bandwidth blocking probability, GSNR, number of LCIs, and modulation cardinality. Finally, we compare the performance of LOGON versus GON strategies at the network-wide level.

A. Physical Layer Parameters for Span-Level and Network-Wide Study

This paper considers an SSF with zero water peak. Fig. 2 depicts the fiber loss profile. The dispersion is calculated based on (6) with $\beta_2 = -21.86 \times 10^{-27} [\text{s}^2 \cdot \text{m}^{-1}]$, $\beta_3 = 0.1331 \times 10^{-39} [\text{s}^3 \cdot \text{m}^{-1}]$, and $\beta_4 = -2.7 \times 10^{-55} [\text{s}^4 \cdot \text{m}^{-1}]$. The measured effective area is illustrated in Fig. 4, and $n_2 = 2.6 \times 10^{-20}$. The characterization of Raman gain profile $C_r(f_p, \Delta f)$ was initially conducted on a SSF and subsequently adjusted in frequency [19]. Fig. 4 illustrates the plot of two instances of $C_r(f_p, \Delta f)$ for 200 THz and 205 THz pump frequencies. The assumption is made that the utilized link incorporates lumped amplifiers, including the following DFAs with their respective noise figures: Erbium DFA (EDFA) at 4.5 dB (C-band), EDFA at 5 dB (L-band), and Thulium DFA at 6 dB (S-band). Additionally, a total of 20 THz ($6 + 6 + 8$) is allocated for the LCS-band scenario [49], with a 400 GHz gap between the bands. Moving forward, we assume that the fixed-grid and flexible bit-rate LCIs operate at 64 Gbaud, with a roll-off factor of 0.05, pre-FEC BER

of 1.5×10^{-2} , and bit rates ranging from 100G to 600G. Therefore, according to [12], the required GSNR, for $m = 1-6$, is 3.45, 6.5, 8.4, 12.4, 16.5, and 19.3 dB, respectively. It is important to emphasize that these assumptions align with state-of-the-art technologies, such as SD-FEC [50]. Consequently, by allocating a 25% overhead for SD-FEC, we can implement fixed-grid and flexible bit-rate LCIs ranging from 100 Gbps to 600 Gbps, whose modulation cardinality can be adjusted and controlled by an SDN controller. In this setup, the channel spacing is set at 75 GHz (6×12.5 GHz).

B. Span-Level Study: FLP Vs. FRP HPO

The span-level analysis forms the foundation of this research. As the span-by-span power optimization is devised according to the LOGON strategy of the network, our initial focus is on demonstrating the performance of FRP and FLP at the span level. Given the constraints of the terrestrial backbone mesh network, where specifying long-haul paths with varying reach distances and considering DGE at specific ILAs is impractical, we assume that all ILAs are equipped with DGE.

According to Algorithm 1, the FLP mode aims to find a flat launch power that maximizes the capacity of each span. Conversely, in the FRP mode, the objective is to find a flat receive power to maximize the capacity of the span. In the former approach, the PEP is computed by solving (10) in the forward mode, while in the latter approach, it is derived by solving (10) in the backward mode. As illustrated in Fig. 4(b), the findings indicate an improvement of about 6.3 Tbps in TC over a 70 km span. In this scenario, we consider a flat received power across all bands. However, an alternative scenario could entail assigning a flat power per band based on the noise figure modification factor.

To gain deeper insights into how FRP can enhance the TC of a span, we have assessed the GSNR and OSNR profiles along with their corresponding statistics, as depicted by the boxplots in Fig. 5. Once again, let us consider a span length of 70 km. As shown in Fig. 5(a), the GSNR improvement of channels in the C- and LC-band scenarios appears negligible. Particularly, the FRP introduces a tilt in the launch power, resulting in a seesaw effect. This means that to maintain a flat receive power, the launch power of higher-frequency channels must be higher than that of lower-frequency channels. Consequently, as demonstrated in [48], the GSNR of lower frequency channels (L-band) decreases, as indicated by the dashed blue curve in the L-band. Conversely, the GSNR of C-band channels increases (dashed blue curve in the C-band). However, there is no significant improvement in GSNR and TC in the C-band and LC-band scenarios when comparing FRP to FLP. Furthermore, as illustrated in Fig. 5(b), an approximate flat OSNR per band can be observed, which is advantageous for operation, administration, and management tasks. The FRP in the LCS-band scenario shows promising results, with a maximum GSNR gain of about 2.5 dB and an OSNR gain of about 6 dB in the S-band. However, while the GSNR of the L-band channels decreases, this reduction, as demonstrated in the network-wide study, does not necessitate a change in the modulation format of the LPs. Furthermore, we observe

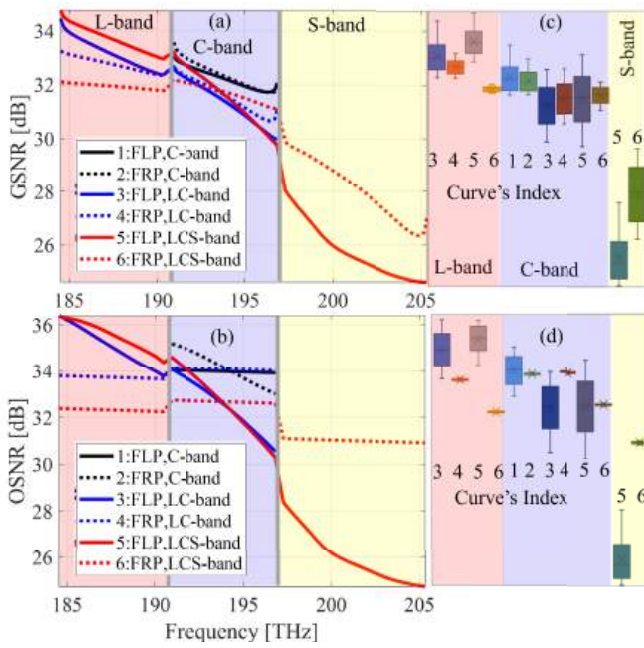


Fig. 5. The single span (a) GSNR profiles and (b) OSNR profiles for FLP and FRP C-band, LC-band, and LCS-band scenarios are depicted. The corresponding box plots are illustrated in (c) and (d) for L-, C-, and S-band. FLP: flat launch power, FRP: flat receive power. The span length is set to $L_s = 70$ km.

an increase in GSNR for the LC-band scenario. This implies that in a pay-as-you-grow migration from the LC band to the LCS band, there is no bit rate penalty for most of the C-band channels. Additionally, we see an approximate OSNR profile for each band. In Figs. 5(a) and (b), there are six curves corresponding to each band and two modes of the HPO algorithm. Boxplots representing these six curves for each band are illustrated in Figs. 5(c) and (d) to demonstrate their sensitivity. The mean (\times), median ($-$), maximum, minimum, and distribution of the channels' GSNR and OSNR are depicted. For instance, as depicted in Figs. 5(c), (e), and (g), FRP not only flattens the GSNR but also significantly improves the GSNR of the S-band channels by about 2.5 dB.

Now, let us evaluate FRP versus FLP for various span lengths. In a real-world network, span lengths vary, leading to differences in physical layer parameters such as amplifier noise figure and loss coefficient, among others, which may change due to aging. This necessitates rapid calculation of the optimum pre-tilt launch power. Additionally, as depicted in Fig. 6 (a), the tilt is not fixed in each band. FRP presents a promising approach to determine the tilt and offset of each band. In the FLP mode, illustrated in Fig. 6 (b), the tilt power is adjusted at the receiver, whereas in the FRP scenario, the tilt launch power is adjusted (Fig. 6 (a)). Once again, we observe the seesaw effect in Fig. 6, where achieving a flat power at the receive side requires increasing the launch power of higher frequency channels. However, considering the dynamic range of DFAs and managing NLI, the maximum launch power has been restricted to 6 dBm [30]. Hence, we observe fewer changes in S-band channels, particularly for distances of 80-100 km. As illustrated in Fig. 6(a), the slope of the tilt in the L-band differs significantly from that of the C- and S-bands. Consequently, the tilt-offset approach proposed in [9]

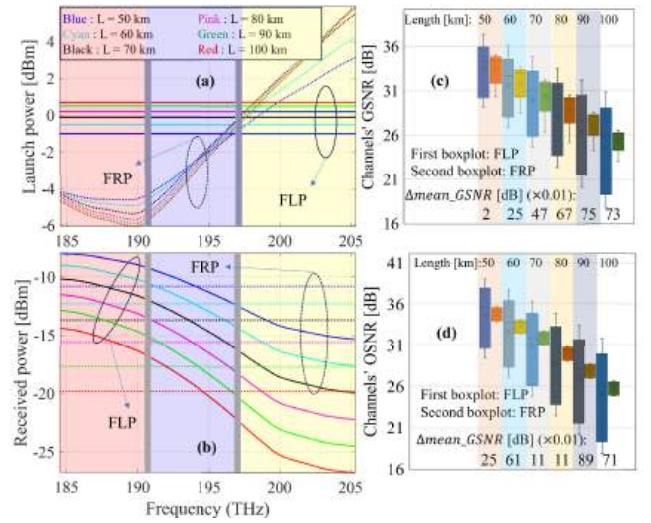


Fig. 6. Power, GSNR, and OSNR profiles comparing flat launch power (FLP) and flat receive power (FRP) for span lengths of 50-100 km. (a) Launch power profile, (b) Received power profile, (c) Box plots of GSNR profiles, and (d) Box plots of OSNR profiles for FLP and FRP.

TABLE II
TOTAL CAPACITY (TC) [TBPS] FOR FLAT LAUNCH POWER (FLP) AND FRP (FLAT RECEIVE POWER) POWER OPTIMIZATION IN TERMS OF SPAN LENGTHS

Length [km]	50	60	70	80	90	100
FLP	445.0	421.8	398.7	375.5	352.0	328.2
FRP	445.3	425.1	405.0	384.6	362.1	337.8
Diff [Tbps]	0.4	3.3	6.3	9.0	10.0	9.7

and [18] becomes highly time-consuming when determining the optimal launch power for live networks, especially when physical parameters of the span are altered. As anticipated, the optimal power also increases with an increase in the span length. The optimal launch powers are within the ranges of $[-0.8, 0.9]$ for FLP and $[-6, 6]$ for FRP. Box plots in Fig. 6 (c) and (d) present the statistical data of channels' GSNR and OSNR for both FLP and FRP, respectively, for each span length. As demonstrated, the gain of FRP over FLP increases with the span length, resulting in up to 6 dB maximum improvements in GSNR and OSNR over a 100 km span. On average, the improvement in GSNR and OSNR is approximately 0.7 dB for a 100 km span. Notably, the QoT gain after 70 km does not change significantly due to the power threshold that has been established.

Subsequently, we present two significant metrics: standard deviation (STD) and the disparity between the maximum and minimum channels' GSNR/OSNR, denoted as Max-Min(GSNR/OSNR). Lower values of STD and Max-Min(GSNR/OSNR) indicate a flatter GSNR/OSNR profile across channels. These flatness indicators are depicted in Fig. 7, where the dashed curves associated with the FRP approach demonstrate lower STD and Max-Min values. Therefore, FRP enhances the average QoT of a span and provides a more uniform GSNR/OSNR profile. Furthermore, Table II presents the TC of spans ranging from 50 to 100 km. It is evident that FRP yields more significant gains for longer span lengths, increasing from 0.4 Tbps for 50 km to approximately 10 Tbps for 100 km.

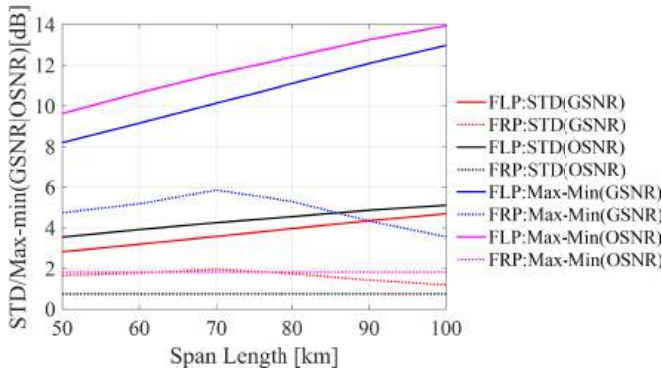


Fig. 7. Standard deviation (STD) and disparity between maximum and minimum channels' GSNR/OSNR for spans of 50–100 km.

C. Network-Wide Study

This section extensively elaborates on comparing the performance between FLP and FRP at the network-wide level. Metrics such as bit-rate blocking probability (BBP), modulation format cardinality usage, average GSNR, and the number of LCIs. The BBP is defined as the sum of the bit rates of the blocked requests over the sum of the bit rates of all the requests processed in the network. The number of LCIs demonstrate the efficiency of each HPO mode.

Moreover, we have examined three networks based on the length of the LPs. These networks include the Spanish backbone (SPNB) with 30 nodes and 56 links, the Japanese backbone (JPNB) with 48 nodes and 82 links, and the United States backbone (USB) with 60 nodes and 79 links, as depicted in Fig. 8. To represent a realistic backbone network planning scenario, we designated specific nodes as the core of the backbone networks. In contrast, the remaining nodes are intermediate nodes equipped solely with ROADMs functionalities without add/drop capabilities. Essentially, these intermediate nodes serve as metro-core nodes, where their traffic is aggregated before reaching the core nodes. This assumption allows us to create a more realistic scenario that accounts for filtering penalties at the intermediate nodes. Accordingly, we refer to the topologies as SPNB3014, JPNB4812, and USB6012. In SPNB, 14 out of 30 serve as core nodes, in JPNB, 12 out of 48, and in USB, 12 out of 60. The total number of bidirectional connections, comprising all source-destination pairs, in each network is calculated as $N(N-1)/2$. The selection of a source-destination pair is based on a biased probability distribution function determined by geographical population and degree number [9]. The box plot illustrating the lengths of the three shortest paths depicted in Fig. 9 (a). In Fig. 9 (a), it is evident that the maximum lengths of connections for SPNB3014 are under 1000 km, for JPNB4812 they are under 2350 km, and for USB6012 they are under 6150 km. The maximum span lengths for SPNB3014, JPNB4812, and USB6012 are 60 km, 80 km, and 100 km, respectively. Nodal degree and span length statistics are depicted in box plots in Fig. 9 (b) and (c). This figure illustrates the importance of considering the ROADM filtering effect and the heterogeneous span lengths in planning, which has been overlooked in the distance adaptive approach. Further details regarding the networks under study in this paper can be found in [51],

[52], and [53] for SPNB3014, JPNB4812, and USB6012, respectively.

1) *Channel-Connection Capacity Profile*: The wavelength-dependent capacity profile of all connections for the first candidate shortest path is illustrated in Fig. 10 (a)-(f) for both FLP and FRP HPO modes across three networks. It is observed that higher modulation cardinality usage occurs in FRP mode for both C- and S-band channels. As discussed later, modulation cardinality ranges from 1 to 6, corresponding to bit rates of 100G to 600G for LCIs, with these values determined based on the GSNR of connections in each band. Fig. 10 demonstrates that the bit rate of an LCI for a connection depends entirely on the channel frequency. Additionally, it can be concluded that in the SPNB3014 and JPN4812 networks, most of the channel-connection resources (CCRs) in the L-band operate at the highest modulation cardinality, maintaining the same bit rate in both FLP and FRP modes. While FRP may degrade the L-band channels, the connection distances and GSNR thresholds remain within safe limits, with no observed bit rate degradation. However, in some instances, such as connection 8 in JPNB4812 and very long-haul connections in USB6012, the bit rate of L-band CCRs in FLP mode may be higher than in FRP mode. Nonetheless, a different behavior is observed concerning C- and especially S-band CCRs. For instance, as illustrated in Fig. 10, there are certain CCRs in the S-band for USB6012 in FLP mode that cannot be utilized due to their GSNR being lower than the minimum GSNR required for the lowest modulation cardinality (as depicted by black markers in Fig. 10 (e)). However, when transitioning to FRP mode, these CCRs survive, albeit with a decrease in bit rate in the L-band (as shown in Fig. 10 (f)). Consequently, the increase in GSNR in the S-band is offset by the decrease in GSNR in the L-band. Notably, the number of CCRs in the S-band exceeds those in the L-band. Therefore, studying FLP and FRP at a network-wide level is imperative to quantify the benefits FRP offers to telecommunication operators (Telcos).

2) *The Networks' Optimal Launch Power Profiles Per Span*: The launch power profile of the FLP and FRP modes are depicted in Fig. 11 (a) and (b) respectively. As anticipated, both the average and range of launch power tend to increase with network size. In the FLP mode (Fig. 11 (a)), the SPNB3014 exhibits a launch power range between -1.5 dBm and -0.5 dBm, the JPN4812 between -1.7 dBm and 0.1 dBm, and the USB6012 between -1.7 dBm and 0.7 dBm. Given that the span length is consistent for each link and we have considered the average span length for each link, the optimal power for each link is reported. In contrast, in the FRP mode, where pre-tilted launch power is employed, the average launch power profiles for all links per network are presented in Fig. 11 (b). The behavior of the launch power profile differs in this case; with increasing network size, the launch power range expands in the S-band but contracts in the C- and L-bands, exhibiting a seesaw effect.

3) *GSNR and Modulation Cardinality Usage*: To comprehensively understand FLP and FRP performance in MB-EONs, it is essential to scrutinize GSNR and modulation cardinality characteristics. Figs 12 (a)-(i) depict GSNR traits for all CCRs, along with modulation cardinality usage and percentage of

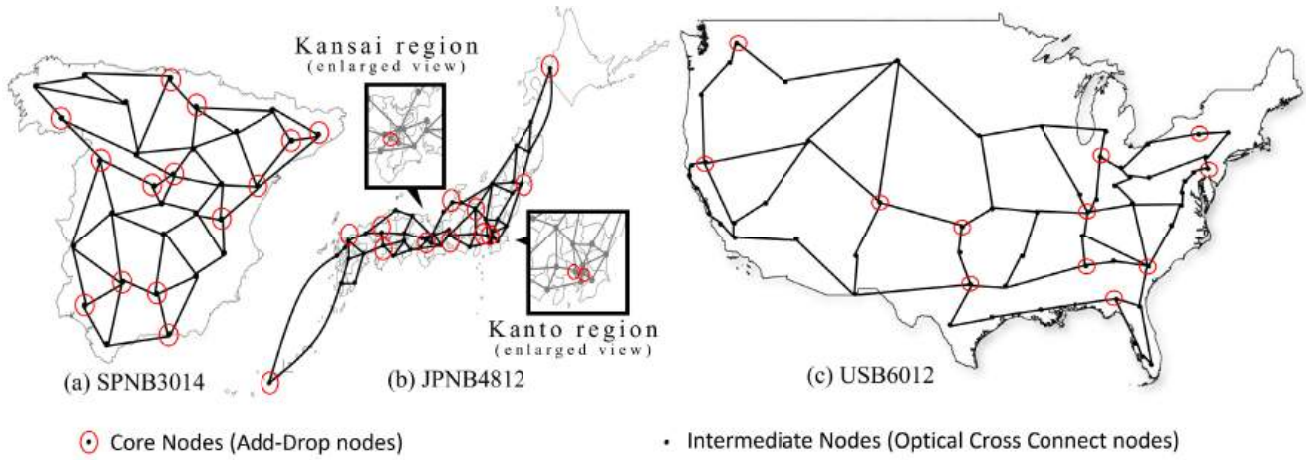


Fig. 8. Network topology of (a) Spanish backbone (SPNB3014), (b) Japanese backbone (JPN4812), and (c) United State backbone (USB6012).

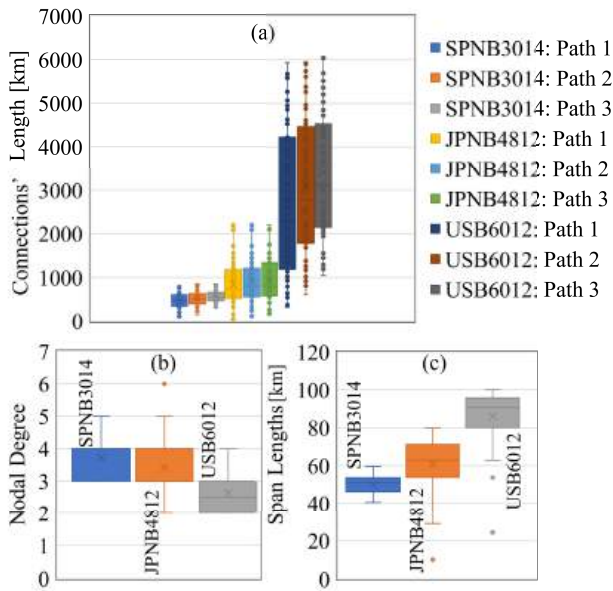


Fig. 9. (a) Connections' length, (b) Nodal degree, and (c) span length of SPNB3012, JPNB4812, and USB6012.

modulation cardinality usage per shortest path for SPNB3014 ((a)-(c)), JPNB4812 ((d)-(f)), and USB6012 ((g)-(i)). Notably, the first box plot in each band corresponds to FLP, while the second represents FRP. Although the average GSNR of L-band CCRs decreases in FRP compared to FL, no modulation cardinality changes are observed in SPNB3014 across all shortest paths (1, 2, and 3). Conversely, JPNB4812 and USB6012 demonstrate distinct trends, showcasing, for instance, a 3 dB average GSNR degradation and 1.3 modulation cardinality changes on average for USB6012, and 1 dB and 1, respectively, for JPNB4812. An intriguing discovery is the comparable performance of FRP and FLP in terms of the average GSNR and modulation cardinality in the C-band across all candidate paths. FRP exhibits promising performance in the S-band, enhancing both average GSNR and utilization of higher modulation cardinality. Consequently, CCR capacity increases significantly across all candidate shortest paths, with USB6012 particularly benefiting due to its numerous long-haul connections, such as those spanning the eastern and western

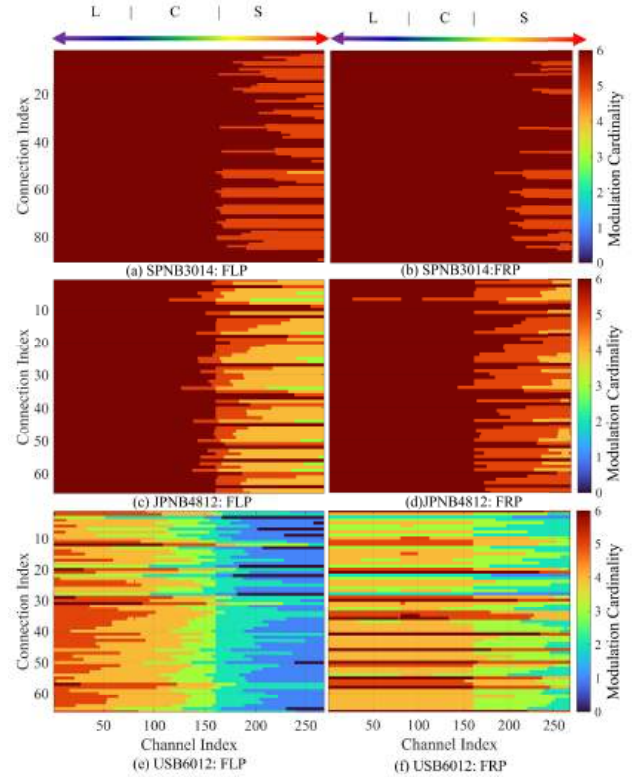


Fig. 10. Channel-connection capacity profile for the first candidate path in (a) SPNB3014-FLP, (b) SPNB3014-FRP, (c) JPNB4812-FLP, (d) JPNB4812-FRP, (e) USB6012-FLP, (f) USB6012-FRP. * to save space, we skip to show the channel-connection capacity profiles of the second and third shortest paths.

coasts of the USA. Notably, FRP enables the survival of previously infeasible CCRs and eliminates CCRs with zero modulation cardinality. Lastly, the percentage of modulation cardinality usage per candidate path, depicted in the last column of Fig. 12, underscores a consistent enhancement in CCRs capacity with significant modulation cardinality changes from lower to higher levels in FRP compared to FLP.

4) *BBP Analysis:* The primary question that often arises is how FRP can potentially decrease the BBP in the network. Answering this question can provide Telcos with valuable insights to make informed decisions between FRP and FLP, potentially reducing the implementation costs of network

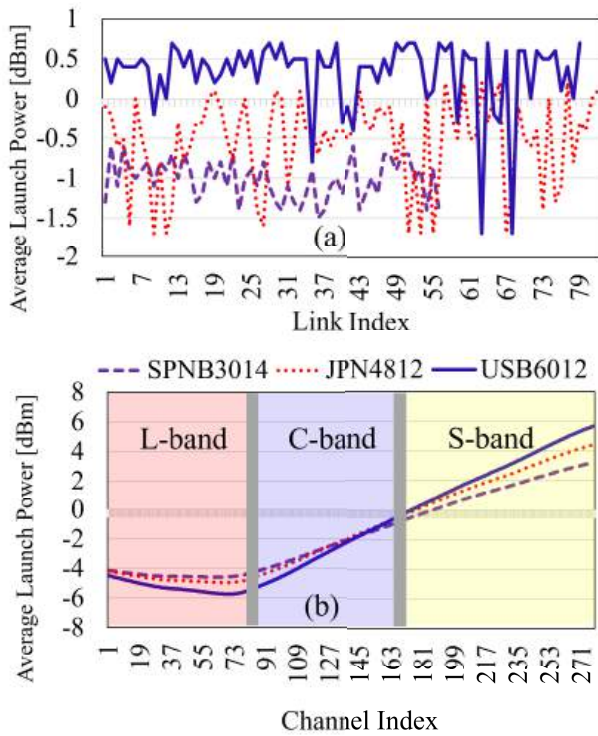


Fig. 11. The average launch power (a) per link is optimized with flat launch power (FLP), and (b) per links and channels is optimized with flat received power (FRP) in SPNB3014, JPN4812, and USB6012.

infrastructure. However, it is worth noting that higher GSNR, especially in the S-band, is guaranteed with FRP, thereby ensuring higher modulation cardinality for CCRs. Based on previous results, we can speculate that FLP might not significantly underperform, depending on the network size. To explore this further, we adopt a semi-static approach, commonly used in backbone networks, where traffic remains in the network for an extended period once it arrives. Our analysis considered $k = 3$ shortest candidate paths for each request. The CCRs were pre-calculated for FLP and FRP modes, with results obtained from 1000 random iterations. The requested bit rate ranged randomly from 100 Gbps to 600 Gbps, with Flexpander grooming taken into account based on Fig. 3. However, it is noted that the authors in [9] and [24] did not consider Flexpander grooming, prompting us to remodel their algorithm accordingly. We implement a minimum LCI deployment algorithm, implying that if sufficient resources are available among the already installed LCIs for a connection, deploying new LCIs is unnecessary. Notably, to minimize jitter, we assume that the flow of each request wholly traverses a single path. Two path selection algorithms are examined: one focuses on maximizing the minimum GSNR of the LCIs, named MaxMinGF [9], [24], while the other aims at minimizing the maximum LCIs' frequency, named MinMaxF [54]. Additionally, three modulation cardinality selection algorithms are explored: channel-based GSNR (CBG), worst case in all bands (WAB), and worst case per band (WPB). In CBG, we evaluate the modulation cardinality for each channel based on channel-connection resources. In WAB [11], [20], [26], a distance adaptive approach is adopted, considering the minimum GSNR across all bands. We employ a similar distance adaptive approach in WPB but focus on the minimum GSNR

within each band for modulation cardinality selection [20], [26].

The results from the BBP are demonstrated in Fig. 13(a)-(c). Since a 1% BBP is deemed acceptable for Telcos, these algorithms are evaluated against BBP 1%. As expected, FRP demonstrates superior performance compared to FLP across all networks. The network throughput gain of FRP over FLP varies depending on the network size, with an approximate gain of 5% observed in all networks under study. Interestingly, despite the increase in average GSNR and CCRs with FRP at both the span and CCR levels, there is no significant enhancement in network throughput in backbone terrestrial networks. Moreover, FRP could be more expensive than the FLP mode due to DGEs and software issues. Hence, this aspect warrants further exploration in future studies, which may be of interest from Telcos' perspective. In conclusion, a maximum 10 Tbps improvement in TC per span may not significantly enhance the total network throughput. Regarding the path selection algorithm, MinMaxF displayed a more significant performance than MaxMinGF, with a notable decrease in spectral fragmentation observed. As anticipated, CBG, based on synergizing the HPO and wavelength-based QoT-aware cross-layer design, demonstrates a network throughput gain of up to 75% at a 1% BBP compared to WAB and WAP.

5) *Local Optimization Versus Global Optimization*: In the latest analysis, we compared the traditional LOGON power optimization and the proposed global power optimization at the network-wide level (GON). While LOGON (optimum power per span) is designed for specific cases in C-band optical networks, its performance, alongside GON, has not been evaluated at the network-wide level in terms of BBP. In the GON approach, we aim for uniform optimal power settings across all spans to enhance network throughput at a given BBP (e.g., 1%). For this study, we employ the FLP mode in USB6012 without loss of generality. As illustrated in Fig. 13(d)-(f), GON with launch powers of 0 and -1 dBm demonstrates comparable performance to FLP LOGON. Given that implementing GON in hardware and software is simpler and potentially more cost-effective than LOGON, GON is recommended. The BBP, LCI usage, and average GSNR of established LPs versus offered traffic load are depicted in Fig. 13 (d)-(f), respectively.

D. HPO Computation Time and Complexity

The runtime of our implementation was measured on a computer equipped with an user-grade Intel Core i7-12700K processor, featuring 4 cores with a base clock of 3.6 GHz. The system had 32 GB of DDR4 RAM running at 3,200 MHz. A 1 TB NVMe SSD was used for storage, ensuring fast read and write operations. The machine ran Microsoft Windows 10, and the HPO algorithm was implemented using MATLAB version R2023a. The runtime for HPO averages to approximately three seconds for span lengths ranging from 50 to 100 km. Based on Alg. 1, the worst-case computational complexity is:

$$O\left(\frac{P_{\text{end}} - P_{\text{start}}}{0.1} \times |C|^2\right), \quad (11)$$

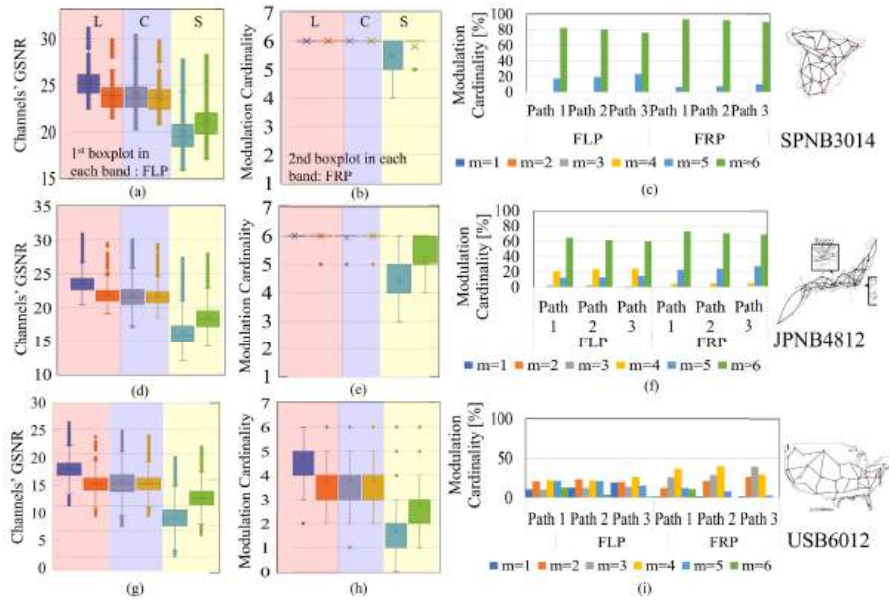


Fig. 12. GSNR and modulation cardinality box plots, and modulation cardinality percentage in each candidate path with FLP and FRP for (a)-(c) SPNB3014, (d)-(f) JPNB4812, and (g)-(i) USB6012.

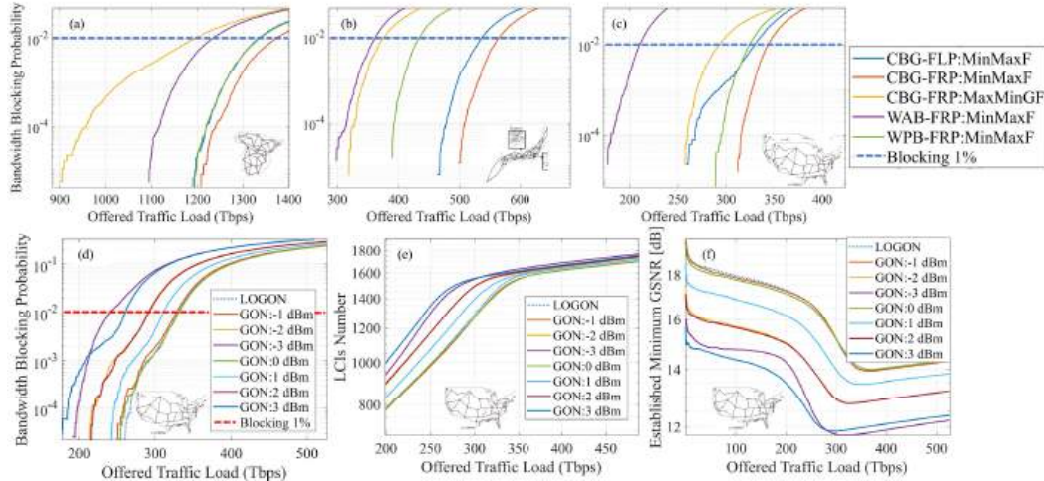


Fig. 13. The bandwidth blocking probability (BBP) v.s offered traffic load (OTL) for different path selection and power optimization methods (a) SPNB3014, (b) JPN4812, and (c) USB6012. The BBP, line card interfaces number, and GSNR v.s OTL for LOGN and GON in (d), (e), and (f), respectively.

where P_{start} and P_{end} represent the range of power to be investigated (Alg. 1, line 3), and \mathcal{C} is the set of channels, with $|\mathcal{C}|^2$ complexity due to line 4 of Alg. 1.

VII. CONCLUSION

The paper explored various power optimization strategies for multi-band elastic optical networks (MB-EONs), focusing on fixed-grid flexible bit rate LCIs capable of adapting to different modulation cardinalities based on the GSNR of the channel. It compares two hyper-accelerated power optimization (HPO) modes based on the local optimization-global optimization (LOGO) concept: flat Receive Power (FLR) and flat Launch Power (FLP). Through exhaustive simulations conducted at both the span and network-wide levels, the study reveals that while FRP introduces greater total capacity in terms of span-level and channel-connection resources, its performance does not significantly outperform FLP across networks of varying sizes. The network gain

achieved by FRP versus FLP is approximately 5%. Additionally, a wavelength-dependent QoT-aware modulation format cardinality assignment model, termed channel-based GSNR, demonstrates up to a 75% higher network throughput compared to previously proposed worst-case scenarios. Lastly, the study indicates that employing identical power settings for all spans named global optimization of the network yields similar performance in terms of maximum network throughput at a fixed BBP in the network-wide analysis. This paper serves as a benchmark and provides valuable insights for telecommunication operators considering power optimization strategies when transitioning from C-band to beyond-C-band networks. Although the physical layer model adopted in this paper can be applied to the ultra-wide-band (L+C+S+E+O) EON scenario, the complexity of QoT estimation increases substantially compared to the C+L+S scenario considered in this paper. A potential solution to this problem is use machine learning to accelerate the QoT estimation, while applying HPO for the power optimization.

REFERENCES

- [1] A. Souza et al., "Cost analysis of ultrawideband transmission in optical networks," *J. Opt. Commun. Netw.*, vol. 16, no. 2, p. 81, Feb. 2024.
- [2] J. P. Fernández-Palacios, F. Arpanaei, J. M. Rivas-Moscote, J. A. Hernández, and D. Larrabeiti, "Investigation of mid-term migration scenarios to multi-band solutions in metropolitan networks," in *Proc. 23rd Int. Conf. Transparent Opt. Netw. (ICTON)*, Jul. 2023, pp. 1–4.
- [3] R. K. Jana, A. Srivastava, A. Lord, and A. Mitra, "Optical cable deployment versus fiber leasing: An operator's perspective on CapEx savings for capacity upgrade in an elastic optical core network," *J. Opt. Commun. Netw.*, vol. 15, no. 8, pp. C179–C191, Aug. 2023.
- [4] T. Hoshida et al., "Ultrawideband systems and networks: Beyond C+L-band," *Proc. IEEE*, vol. 110, no. 11, pp. 1725–1741, Nov. 2022.
- [5] G. Bennett, *More Capacity? No Problem With Hitless C+L Expansion*. Accessed: Feb. 22, 2025. [Online]. Available: <https://www.infinera.com/blog/more-capacity-no-problem-with-hitless-cl-expansion-b/tag/submarine/>
- [6] D. Semrau, E. Sillekens, R. I. Killey, and P. Bayvel, "A modulation format correction formula for the Gaussian noise model in the presence of inter-channel stimulated Raman scattering," *J. Lightw. Technol.*, vol. 37, no. 19, pp. 5122–5131, Oct. 1, 2019.
- [7] D. Semrau, E. Sillekens, P. Bayvel, and R. I. Killey, "Modeling and mitigation of fiber nonlinearity in wideband optical signal transmission [invited]," *J. Opt. Commun. Netw.*, vol. 12, no. 6, pp. C68–C76, Jun. 2020.
- [8] S. Escobar-Landero, A. Lorences-Riesgo, X. Zhao, Y. Frignac, and G. Charlet, "S+C+L high-capacity transmission systems: Challenges and opportunities," *J. Lightw. Technol.*, vol. 42, no. 12, pp. 4260–4270, Jun. 15, 2024.
- [9] B. Correia et al., "Power control strategies and network performance assessment for C+L+S multiband optical transport," *J. Opt. Commun. Netw.*, vol. 13, no. 7, pp. 147–157, Jul. 2021.
- [10] F. Arpanaei et al., "Hyperaccelerated power optimization in multi-band elastic optical networks," in *Proc. Opt. Fiber Commun. Conf. (OFC)*, 2024, pp. 1–3.
- [11] N. Sambo et al., "Provisioning in multi-band optical networks," *J. Lightw. Technol.*, vol. 38, no. 9, pp. 2598–2605, May 30, 2020.
- [12] F. Arpanaei et al., "Enabling seamless migration of optical metro-urban networks to the multi-band: Unveiling a cutting-edge 6D planning tool for the 6G era," *J. Opt. Commun. Netw.*, vol. 16, no. 4, p. 463, 2024.
- [13] C. Lasagni, P. Serena, A. Bononi, and J.-C. Antona, "Power allocation optimization in the presence of stimulated Raman scattering," in *Proc. Eur. Conf. Opt. Commun. (ECOC)*, Sep. 2021, pp. 1–4.
- [14] A. Souza et al., "Optimal pay-as-you-grow deployment on S+C+L multi-band systems," in *Proc. Opt. Fiber Commun. Conf. Exhib. (OFC)*, Mar. 2022, pp. 1–3.
- [15] A. Souza, N. Costa, J. Pedro, and J. Pires, "Service-aware genetic algorithm for link power control in multi-band optical transmission systems," in *Proc. Eur. Conf. Opt. Commun. (ECOC)*, Sep. 2022, pp. 1–4.
- [16] I. Roberts, J. M. Kahn, J. Harley, and D. W. Boertjes, "Channel power optimization of WDM systems following Gaussian noise nonlinearity model in presence of stimulated Raman scattering," *J. Lightw. Technol.*, vol. 35, no. 23, pp. 5237–5249, Dec. 9, 2017.
- [17] H. Buglia, E. Sillekens, A. Vasylenkova, P. Bayvel, and L. Galdino, "On the impact of launch power optimization and transceiver noise on the performance of ultra-wideband transmission systems [Invited]," *J. Opt. Commun. Netw.*, vol. 14, no. 5, pp. B11–B21, May 2022.
- [18] H. Luo, J. Lu, Z. Huang, C. Yu, and C. Lu, "Optimization strategy of power control for C+L+S band transmission using a simulated annealing algorithm," *Opt. Exp.*, vol. 30, no. 1, pp. 664–675, Jan. 2022.
- [19] P. Poggiolini and M. Ranjbar-Zefreh, "Closed form expressions of the nonlinear interference for UWB systems," in *Proc. Eur. Conf. Opt. Commun. (ECOC)*, Sep. 2022, pp. 1–4.
- [20] M. Mehrabi, H. Beyranvand, and M. J. Emadi, "Multi-band elastic optical networks: Inter-channel stimulated Raman scattering-aware routing, modulation level and spectrum assignment," *J. Lightw. Technol.*, vol. 39, no. 11, pp. 3360–3370, Jun. 1, 2021.
- [21] Q. Yao et al., "SNR re-verification-based routing, band, modulation, and spectrum assignment in hybrid C–C+L optical networks," *J. Lightw. Technol.*, vol. 40, no. 11, pp. 3456–3469, Jun. 3, 2022.
- [22] P. Poggiolini, "A generalized GN-model closed-form formula," 2018, *arXiv:1810.06545*.
- [23] M. R. Zefreh and P. Poggiolini, "A real-time closed-form model for non-linearity modeling in ultra-wide-band optical fiber links accounting for inter-channel stimulated Raman scattering and co-propagating Raman amplification," 2020, *arXiv:2006.03088*.
- [24] R. K. Jana et al., "Quality-aware resource provisioning for multiband elastic optical networks: A deep-learning-assisted approach," *J. Opt. Commun. Netw.*, vol. 14, no. 11, pp. 882–893, Nov. 2022.
- [25] Y. Song, Q. Fan, C. Lu, D. Wang, and A. P. T. Lau, "Efficient three-step amplifier configuration algorithm for dynamic C+L-band links in presence of stimulated Raman scattering," *J. Lightw. Technol.*, vol. 41, no. 5, pp. 1445–1453, Mar. 23, 2023.
- [26] F. Calderón et al., "Heuristic approaches for dynamic provisioning in multi-band elastic optical networks," *IEEE Commun. Lett.*, vol. 26, no. 2, pp. 379–383, Feb. 2022.
- [27] Y. Jiang et al., "Performance enhancement of long-haul C+L+S systems by means of CFM-assisted optimization," in *Proc. Opt. Fiber Commun. Conf. (OFC)*, San Diego, CA, USA, 2024, p. 1.
- [28] P. Poggiolini, G. Bosco, A. Carena, V. Curri, Y. Jiang, and F. Forghieri, "The GN-model of fiber non-linear propagation and its applications," *J. Lightw. Technol.*, vol. 32, no. 4, pp. 694–721, Feb. 17, 2014.
- [29] D. J. Ives, P. Bayvel, and S. J. Savory, "Adapting transmitter power and modulation format to improve optical network performance utilizing the Gaussian noise model of nonlinear impairments," *J. Lightw. Technol.*, vol. 32, no. 21, pp. 4087–4096, Nov. 8, 2014.
- [30] L. Rapp and M. Eiselt, "Optical amplifiers for multi-band optical transmission systems," *J. Lightw. Technol.*, vol. 40, no. 6, pp. 1579–1589, Mar. 15, 2022.
- [31] F. Arpanaei, N. Ardalani, H. Beyranvand, and B. Shariati, "QoT-aware performance evaluation of spectrally-spatially flexible optical networks over FM-MCFs," *J. Opt. Commun. Netw.*, vol. 12, no. 8, pp. 288–300, Aug. 2020.
- [32] A. Lord, P. Wright, and A. Mitra, "Core networks in the flexgrid era," *J. Lightw. Technol.*, vol. 33, no. 5, pp. 1126–1135, Mar. 1, 2015.
- [33] D. G. Sequeira, L. G. Cancela, and J. L. Rebola, "Impact of physical layer impairments on multi-degree CDC ROADM-based optical networks," in *Proc. Int. Conf. Opt. Netw. Design Model. (ONDM)*, May 2018, pp. 94–99.
- [34] J. Pedro, N. Costa, and S. Sanders, "Cost-effective strategies to scale the capacity of regional optical transport networks," *J. Opt. Commun. Netw.*, vol. 14, no. 2, pp. A154–A165, Feb. 2022.
- [35] D. Zhang et al., "Technological prospection and requirements of 800G transmission systems for ultra-long-haul all-optical terrestrial backbone networks," *J. Lightw. Technol.*, vol. 41, no. 12, pp. 3774–3782, Jun. 15, 2023.
- [36] H. Lun et al., "Machine-learning-based telemetry for monitoring long-haul optical transmission impairments: Methodologies and challenges [invited]," *J. Opt. Commun. Netw.*, vol. 13, no. 10, pp. E94–E108, Oct. 2021.
- [37] T. Tanaka, T. Inui, S. Kawai, S. Kuwabara, and H. Nishizawa, "Monitoring and diagnostic technologies using deep neural networks for predictive optical network maintenance [invited]," *J. Opt. Commun. Netw.*, vol. 13, no. 10, pp. E13–E22, Oct. 2021.
- [38] P. Poggiolini and Y. Jiang, "Recent advances in the modeling of the impact of nonlinear fiber propagation effects on uncompensated coherent transmission systems," *J. Lightw. Technol.*, vol. 35, no. 3, pp. 458–480, Feb. 1, 2017.
- [39] H. Buglia et al., "A closed-form expression for the Gaussian noise model in the presence of inter-channel stimulated Raman scattering extended for arbitrary loss and fibre length," *J. Lightw. Technol.*, vol. 41, no. 11, pp. 3577–3586, Nov. 13, 2023.
- [40] A. D'Amico et al., "Scalable and disaggregated GGN approximation applied to a C+L+S optical network," *J. Lightw. Technol.*, vol. 40, no. 11, pp. 3499–3511, Jun. 1, 2022.
- [41] D. Uzunidis, E. Kosmatos, C. Matrakidis, A. Stavdas, and A. Lord, "Strategies for upgrading an operator's backbone network beyond the C-band: Towards multi-band optical networks," *IEEE Photon. J.*, vol. 13, no. 2, pp. 1–18, Apr. 2021.
- [42] A. Souza, N. Costa, J. Pedro, and J. Pires, "Comparison of fast quality of transmission estimation methods for c + l + s optical systems," *J. Opt. Commun. Netw.*, vol. 15, no. 11, pp. F1–F12, 2023.
- [43] C. Lasagni, P. Serena, A. Bononi, and J.-C. Antona, "A generalized Raman scattering model for real-time SNR estimation of multi-band systems," *J. Lightw. Technol.*, vol. 41, no. 11, pp. 3407–3416, Nov. 1, 2023.

- [44] V. Curri, "GNPy model of the physical layer for open and disaggregated optical networking [invited]," *J. Opt. Commun. Netw.*, vol. 14, no. 6, pp. C92–C104, Jun. 2022.
- [45] Y. Jiang et al., "Experimental test of a UWB closed-form EGN model," in *Proc. IEEE Photon. Conf. (IPC)*, Nov. 2023, pp. 1–2.
- [46] Infinera. (2024). *Packet Optical: The Infinera Way*. Accessed: Sep. 17, 2024. [Online]. Available: <https://www.infinera.com/e-book/packet-optical-the-infinera-way/>
- [47] V. Curri, "Multiband optical transport: A cost-effective and seamless increase of network capacity," in *Proc. OSA Adv. Photon. Congr.*, 2021.
- [48] F. Arpanaei et al., "Launch power optimization for dynamic elastic optical networks over C+L-bands," in *Proc. Int. Conf. Opt. Netw. Design Model. (ONDM)*, 2023.
- [49] Ciena. (2021). *A Model for Bus. Case Analysis C/L-Band Netw. Architectures Fiber Optic Network Based Leased/irru Dark Fiber*. [Online]. Available: <https://www.ciena.com/insights/white-papers/a-model-for-business-case-analysis-of-c-l-band-network-architectures.html>
- [50] A. Alvarado, D. J. Ives, S. J. Savory, and P. Bayvel, "On the impact of optimal modulation and FEC overhead on future optical networks," *J. Lightw. Technol.*, vol. 34, no. 9, pp. 2339–2352, May 13, 2016.
- [51] Telefonica. (2015). *Industry-driven Elastic and Adaptive Lambda Infrastructure for Service and Transport Networks*. [Online]. Available: <https://cordis.europa.eu/project/id/317999>
- [52] IEICE. (2021). *Japan Photonic Network Model*. [Online]. Available: <https://www.ieice.org/>
- [53] J. M. Simmons, *Optical Network Design and Planning (Optical Networks)*, 2nd ed., Cham, Switzerland: Springer, 2014.
- [54] F. Arpanaei, J. M. Rivas-Moscoso, M. R. Zefreh, J. A. Hernández, J. P. Fernández-Palacios, and D. Larrabeiti, "A comparative study on routing selection algorithms for dynamic planning of EONs over C+L bands," in *Proc. Adv. Photon. Congr.*, 2023.

Yanchao Jiang (Member, IEEE) received the Ph.D. degree in electronics and telecommunications from the Politecnico di Torino, Italy. She is currently a Post-Doctoral Researcher with the Politecnico di Torino. Her research focuses on optical communications, specializing in modeling fiber nonlinearity in ultra-wideband systems.

Pierluigi Poggiolini (Fellow, IEEE) received the M.S. (cum laude) and Ph.D. degrees from the Politecnico di Torino, Italy. From 1988 to 1989, he was with Italian State Telephone Company Research Center CSELT, Turin. From 1990 to 1995, he was a Visiting Scholar and then a Post-Doctoral Fellow with Stanford University. Since 1995, he has been with the Politecnico di Torino and in 2010, he became a Full Professor in optical communications. His current research interests focus on the modeling of non-linear fiber effects and on ultra-wide-band coherent transmission systems over both conventional and hollow-core fibers. He was an elected member of the Academic Senate (2005–2010) and an elected member of the Board of Directors (2016–2020) of the Politecnico di Torino. He was the Technical Co-Chair of the ECOC Conference in 2010. He has published 300 papers in leading journals and conferences. His papers have received more than 11 000 citations. He is the co-author of two papers, published in 2011 and 2012, that have received the "Journal of Lightwave Technology Best Paper Award." He is a fellow of Optica and appears in the top 1% on Stanford University's worldwide researchers list (2024 edition).

Kimia Ghodsifar received the M.S. degree from the Amirkabir University of Technology (Tehran Polytechnic), Tehran, Iran, in 2023. She is currently pursuing the Ph.D. degree with the University of Waterloo, Canada. She was working at the Amirkabir University of Technology.



Farhad Arpanaei (Member, IEEE) received the Ph.D. degree (Hons.) in electrical engineering, specializing in telecommunications systems from Central Tehran Azad University, Tehran, Iran, in 2019. He is currently a Researcher with the Universidad Carlos III de Madrid (UC3M), Spain, where he held a Marie Skłodowska-Curie (MSCA) Post-Doctoral Fellowship from September 2021 to September 2024. As part of this fellowship, he conducted research visits with Telefónica, Spain, and Chalmers University of Technology, Sweden. Prior to joining UC3M, he was a Post-Doctoral Researcher with the Polytechnic University of Turin, Italy, in 2021. From July 2013 to January 2021, he was an Optical Network Engineer with Telecommunication Infrastructure Company (TIC), Tehran. His research interests include QoT-aware cross-layer design of SDN-assisted optical networks over multi-band and/or SDM systems, with a focus on optimization and AI/ML algorithms. He also serves as a reviewer for several highly ranked IEEE and Optica journals, such as JLT, JOCN, IEEE JOURNAL ON SELECTED AREAS IN COMMUNICATIONS, *Optics Express*, IEEE COMMUNICATIONS LETTERS, and IEEE ACCESS.



Hamzeh Beyranvand received the M.Sc. and Ph.D. degrees from the Sharif University of Technology (SUT), Tehran, Iran, in 2008 and 2014, respectively. He was a Visiting Associate Researcher with the Institut National de la Recherche Scientifique, Montreal, Canada, from 2013 to 2014. He has been with the Department of Electrical Engineering, Amirkabir University of Technology (Polytechnic of Tehran), Tehran, since 2015, where he is currently an Associate Professor. His research focuses on fiber optic communications, optical wireless communications, broadband access networks, and network planning and optimization. He has received several awards, including the 14th Iran National Khwarizmi Youth Award in 2012, the Outstanding Ph.D. Student Award from SUT in 2013, the IEEE Iran Section Best Ph.D. thesis Award in 2015, and the FQRNT Post-Doctoral Fellowship from the Quebec Government in 2015. In 2024, he was named Distinguished Young Researcher in Electrical Engineering by the Academy of Sciences of Iran.



Mahdi Ranjbar Zefreh received the Ph.D. degree in electrical engineering, with a focus on optical fiber communication systems from the Sharif University of Technology, Tehran, Iran, in 2015. He is currently an Optical Fiber Engineer and a Researcher with Cisco Systems, Italy, where he focuses on the design and modeling of optical fiber systems. He was a Post-Doctoral Researcher with the Politecnico di Torino and Sharif University of Technology, where his research concentrated on nonlinear interference modeling in coherent WDM systems.



Carlos Natalino (Member, IEEE) received the Ph.D. degree in electrical engineering from the Federal University of Pará, Brazil, in 2016. He is currently a Researcher with the Optical Networks Unit, Chalmers University of Technology. His research focuses on network automation and on the challenges and opportunities for application of machine learning in the network automation context. Over the past years, he has been researching how to leverage machine learning for optical network design and operation, in problems such as resource efficiency (e.g., spectrum) and physical layer security. He has been involved in several national and international projects funded by research bodies in EU, Sweden, and Brazil. He is a member of Optica.



Paolo Monti (Senior Member, IEEE) is currently a Professor and the Head of the Optical Networks Unit, Chalmers University of Technology, where his research focuses on the design and operation of communication infrastructures with an emphasis on energy efficiency, resiliency, programmability, automation, and techno-economics. He has led or contributed to numerous national and international projects funded by prominent research bodies in the EU, USA, and Asia, serving as a principal investigator (PI), a co-principal investigator (Co-PI),

and/or the main technical leader. Currently, he coordinates the Horizon EU SNS-JU Project ECO-eNET, which explores network confluence. His current research interests lie at the intersection of architectural design, technological innovation, programmability, and sustainability challenges in beyond 5G (B5G) and 6G network infrastructures. He regularly serves on the technical program committees of leading IEEE and OSA conferences, including IEEE Globecom, IEEE ICC, and OFC, where he was the N3 and Demo Track Chair. He has also been the General Chair of ONDM 2021; the ONS Symposium Chair of IEEE Globecom 2017; and the TPC Chair of IEEE HPSR 2017, IEEE OnlineGreenComm 2016, and ONDM 2014.



Antonio Napoli received the Ph.D. degree from the Politecnico di Torino. He was with Siemens, NSN, and Coriant in 2006, 2007, and 2013, respectively. Since 2018, he has been with Infinera, where he is currently the Director of hardware development and leads the Strategy and Architecture Engineering Team. He served as an OFC TPC member from 2017 to 2019. He has been a Guest Editor three times of JOCN and JLT. He has been a principal investigator for Infinera in many EU-funded projects: IDEALIST, B5G-OPEN, ALLEGRO, SEASON, and

PROTEUS-6G; and five Marie Skłodowska-Curie Actions (REAL-NET, WON, MENTOR, EMPOWER-6G, and NESTOR). He has co-authored seven patents, more than 250 peer-reviewed articles, and one book chapter. His research interests include coherent point-to-multipoint optical networks, digital signal processing, wideband optical systems, transmission modeling, and ML/AI for optics.

José M. Rivas-Moscó is currently with Telefónica Global CTIO, Madrid, Spain.

Óscar González de Dios is currently with Telefónica Global CTIO, Madrid, Spain.



Juan Pedro Fernández-Palacios received the M.S. degree in telecommunications engineering from the Polytechnic University of Valencia in 2000. In September 2000, he joined Telefonica I+D, where his research activities, where focused on the design of new data and control plane architectures for IP over optical networks. He is the author of six patents filled in Europe and U.S. and more than 70 publications in conferences and journals. He was a Coordinator of two European research projects on optical transport networks (MAINS and IDEALIST)

between 2011 and 2014. In 2013, he joined the Telefonica Global CTO Office as the Head of Transport. In 2016, he also took this position in Telefonica-O2 Germany. From June 2017 to March 2020, he was in charge of the Integrated Transport Centre, a global organization in Telefonica in charge of defining the strategic network planning for IP, DWDM, MW, and satellite networks in Argentina, Chile, Peru, Colombia, and Brazil. Since 2019, he has been responsible for transport technology in GCTIO and leading iFUSION project for common and vendor agnostic transport SDN deployment in IP, optical, and MW networks within Telefonica Group. Currently, he is co-chairing the MUST and TFS groups within the Telecom Infra Project and ETSI, respectively.



Octavia A. Dobre (Fellow, IEEE) is currently a Professor and the Tier-1 Canada Research Chair with Memorial University, Canada. She was a Visiting Professor with Massachusetts Institute of Technology, USA, and Université de Bretagne Occidentale, France. Her research interests encompass wireless communication and networking technologies and optical and underwater communications. She has (co-)authored over 500 refereed articles in these areas. She serves as the VP Publications for the IEEE Communications Society. She was the Inaugural

Editor-in-Chief (EiC) of the IEEE OPEN JOURNAL OF THE COMMUNICATIONS SOCIETY and the EiC of the IEEE COMMUNICATIONS LETTERS. She was a Fulbright Scholar, a Royal Society Scholar, and a Distinguished Lecturer of the IEEE Communications Society. She obtained seven IEEE Best Paper Awards, including the 2024 Heinrich Hertz Award. She is an elected member of the European Academy of Sciences and Arts; and a fellow of the Engineering Institute of Canada, Canadian Academy of Engineering, and the Royal Society of Canada.



José Alberto Hernández (Member, IEEE) received the degree in telecommunications engineering from the Universidad Carlos III de Madrid, Madrid, Spain, in 2002, and the Ph.D. degree in computer science from Loughborough University, Leics, U.K., in 2005. Between 2005 and 2009, he was a Post-Doctoral Researcher and a Teaching Assistant with the Universidad Autónoma de Madrid, where he participated in a number of both national and European research projects concerning the modeling and performance evaluation of communication

networks, optical WDM networks, and energy efficiency in computer communications. Currently, he is a Senior Lecturer with the Universidad Carlos III de Madrid, he has published more than 200 scientific articles in well-known journals and conference proceedings, including *IEEE Network*, *IEEE Communications Magazine*, *IEEE JOURNAL ON SELECTED AREAS IN COMMUNICATIONS*, and *IEEE INTERNET COMPUTING*. He has also participated in many national and European research projects related with his main research interests, namely optical WDM networks, 5G/6G networks, and AI/ML applications to networking. He has also published two books on queueing theory and prompt engineering for generative AI.



David Larrabeiti has been a Professor in switching and network architectures with the Universidad Carlos III de Madrid since 1998. He has participated in a number of EU research projects on next generation optical networks, like the Networks of Excellence e-Photon/One, e-Photon/One+, BONE, the H2020 Project PASSION and 5G-PPP Projects 5G-CrossHaul, and BlueSPACE. His research interests include fast switching technologies, optical networks, and cybersecurity in networking. He is currently participating in EU Horizon Programme

FLEX-SCALE and PROTEUS-6G Projects. He has been a TPC Member of ECOC; the TPC Co-Chair of ONDM2021 and ONDM2023; and the General Chair of ONDM2024.