

General Instantaneous Dynamic Phasor

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Abstract—Dynamic phasor has now been widely used in the fields of ac power and signal, such as power electronics, power systems engineering, and instrumentation. It is, however, broadly misunderstood by users that the dynamic phasor is valid for an averaged period of time. This misbelief stems from the definition of Fourier series coefficients for a variable where the time sliding integration is taken over a period to get its average. In this article, it is verified that the dynamic phasor is valid instantaneously for any time and that averaging over a period has nothing to do with the dynamics of phasor variables. An extended phasor transformation is newly proposed as a generalized instantaneous dynamic phasor. This instantly valid dynamic phasor is thoroughly verified by mathematics, simulation, and experiments. The instantaneous dynamic phasor is found to be valid for an arbitrary and even time-varying frequency, which is not necessarily the same as the source frequency. The transfer function of the phasor space system is found to be a frequency shift form of the original one of the real space system for the fixed frequency dynamic phasor.

Index Terms—Dynamic phasor, generalized averaging, instantaneous dynamic phasor, Laplace transform, phasor transformation.

I. INTRODUCTION

NOWADAYS ‘dynamic phasor’ is quite widely used in the fields of ac power and signal. It is a simple and powerful tool to deal with time-varying ac power and signals. More specifically, the envelope behavior of a sinusoidal waveform can be analyzed by the dynamic phasor. It would be useful for readers to briefly review the history of the dynamic phasor, highlighting a few monument papers.

The phasor concept was first adopted in electrical engineering in 1894 as of the static phasor form [1]. Although this was introduced in electrical engineering, it is applicable to all engineering

and science areas, considering its mathematical formulation. Static phasor has been widely used for the steady-state analyses of ac power, communications, controls, and signal processing. There is so much literature that they are intentionally not provided here to highlight important references only.

So far as we have investigated, the dynamic phasor concept was first adopted in 1961, where the slowly varying phase and amplitude of a variable were examined [2]. Although not called “dynamic phasor” at that time, this concept evolved to “describing function technique” in 1968, where a dynamic phasor form solution is assumed for the analysis of transient oscillation [3]. The dynamic phasor concept presented in [2] and [3] is of a complex form, which neglects the real part operator that connects a real system and its corresponding complex system. There is no equivalent circuit available in the complex domain as well, which is inconvenient for engineers to use in theory. These would be parts of the reasons why there is not many literatures that use this early-stage dynamic phasor.

It was not until 1990 that the modern dynamic phasor became available as the name of “phasor transformation” [4]. A general dynamic phasor concept was proposed, which is instantly valid for any abrupt frequency and phase change of a variable. Dynamically equivalent circuits for *RLC* components, ac voltage/current sources, and ac switching converters in the complex domain are first provided. The real part operator is adopted to retrieve real variables from the complex variables. Thus, the method made it possible to obtain the dynamics of resonant converters with great ease.

A generalized averaging method was proposed in 1991 that applied the describing function technique to converter analysis [5]. This method adopts the Fourier series to represent periodic variables in converters. The time-varying Fourier coefficient is obtained by integrating for a window of length *T* slides over the actual waveform. In this way, the method had successfully expanded the theory of state-space averaging to ac converters. This paper referenced the literature [4] that obtained very similar results of “the time-varying phasor analysis.” Neither equivalent complex circuits nor real part operation were proposed in the generalized averaging method though.

After publications of the two papers, thousands of literatures have addressed dynamic phasor concept [6], [7], [8], [9], [10], [11], [12], [13], [14], [15], [16], [17], [18], [19], [20], which almost refer the two original dynamic phasor papers. Among them, “phasor dynamics” was applied to the analysis of converters in 1993 and 1997, where the convenient real part operation is used and only the fundamental component is considered, truncating all the other harmonics [6], [7]. The exact keyword “dynamic

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phasor” was first used in 1999, whose concept is the same as provided in the previous papers [6], [7], but the name had been changed [8]. So, it is not true that “dynamic phasor was first introduced in 2007” [11], which is 17 years after the first modern dynamic phasor introduction and 8 years after the first use of the same name.

Active societies and journals that use the dynamic phasor concept are found to be power electronics, power systems, instrumentation and measurement, etc. Some of them are reviewing and referencing publications of other areas; however, many of them still exchange information within their own areas and do not even use the dynamic phasor method, although highly needed. The merits and limitations of the dynamic phasor are often not clearly addressed.

One of the widely misunderstood facts is that a dynamic phasor is valid only when the variable is averaged over a period T . This misbelief stems from the definition of Fourier series coefficients for a variable where the time sliding integration is taken over a period to get its average. In this article, it is verified that the dynamic phasor is valid instantaneously for any time and that averaging over a period has nothing to do with the dynamics of phasor variables. This instantly valid dynamic phasor is generally verified by mathematics, simulation, and experiments throughout this article.

II. THEORY ON INSTANTANEOUS DYNAMIC PHASOR

Since most dynamic phasor papers originate from the two original dynamic phasor papers, the “phasor transformation [4]” and “generalized averaging method [5]” are retrieved, interpreted, and compared with each other to make the concept of “instantaneous dynamic phasor” clear. An extended phasor transformation as a generalized instantaneous dynamic phasor is introduced here. As this is not a review article, new aspects of the two dynamic phasor techniques, which are not well known, are to be highlighted.

A. Proposed Extended Phasor Transformation

The representation of the general unified phasor transformation [15] is retrieved here in the standard form, which is the non-rms value of a variable $x(t)$, as follows:

$$x(t) = \text{Re} \left\{ \frac{1}{\sqrt{m}} \mathbf{x}(t) e^{j\theta(t)} \right\} \text{ for } -\infty < t < \infty \quad (1)$$

where $\mathbf{x}(t)$ is the corresponding complex variable, $\theta(t)$ is an arbitrary nonzero phase angle, and m is the number of poly phases, i.e., $m = 1$ for single phase and $m = 3$ for three phase. Note that originally $\theta(t) = \omega_s t$ [4] and it is here extended to an arbitrary phase angle. This phasor transformation of (1) had unified the three-phase case to the single-phase transformation [4] and generalized to an arbitrary frequency and phase case in this article. Because this aspect is important for the proposed instantaneous dynamic phasor, it is explained in detail.

It should be noted from (1) that $\theta(t)$ is not necessarily linear to time t but nonlinear to t ; so, it could be a square wave or

frequency modulation (FM) signal as follows:

$$\theta(t) = \omega_0 t + \alpha \sin \omega_1 t \quad (2)$$

where ω_0, ω_1 , and α are arbitrary constant values. Moreover, $\theta(t)$ is not necessarily a continuous waveform but a discontinuous waveform, such as a step function and a delta function. So, $e^{j\theta(t)}$ is not necessarily a periodic function. Under these severely changing extreme conditions of $\theta(t)$, (1) is still valid for all the time. This means that $\mathbf{x}(t)$ always exist for any $x(t)$ and vice versa, which shall be more rigorously verified in the following. For practical utility, $\theta(t)$ should be chosen to simplify the resulting system equations, reflect the dominant frequency content of the signal, and ensure that the corresponding phasor $\mathbf{x}(t)$ varies as slowly as possible over time.

It is straightforward that $x(t)$ exists for any $\mathbf{x}(t)$ from (1). The reverse, however, is not true. In general, a complex variable $\mathbf{x}(t)$ is composed of its magnitude and phase terms as $|\mathbf{x}(t)|e^{j\angle\mathbf{x}(t)}$; therefore, it can be represented as an example, for a given $x(t)$, as follows:

$$\mathbf{x}(t) = \sqrt{m}x(t) e^{-j\theta(t)}. \quad (3)$$

Then, applying (3) to (1) becomes

$$x(t) = \text{Re} \left\{ \frac{1}{\sqrt{m}} \sqrt{m}x(t) e^{-j\theta(t)} e^{j\theta(t)} \right\} = x(t). \quad (4)$$

For an example of an extreme case, (3) can be found for a unit step function $u(t)$ of $x(t)$ and $\theta(t)$ of (2) as follows:

$$\mathbf{x}(t) = \sqrt{m}u(t) e^{-j(\omega_0 t + \alpha \sin \omega_1 t)}. \quad (5)$$

As identified from (5), $\mathbf{x}(t)$ is neither a stationary phasor nor a slowly varying continuous variable in time.

The time derivative of (1) becomes as follows:

$$\dot{x}(t) = \text{Re} \left[\frac{1}{\sqrt{m}} \left\{ \dot{\mathbf{x}}(t) + j\dot{\theta}(t) \mathbf{x}(t) \right\} e^{j\theta(t)} \right] \quad (6)$$

where the arbitrary phase $\theta(t)$ assumed to be differentiable.

Note that the phasor transformation of (1) and (3) has nothing to do with the Fourier series; therefore, no averaging of $x(t)$ over a period of T is needed.

As identified from (4), $x(t)$ and $\mathbf{x}(t)$ are in 1-to-1 mapping relationship at all times so far as (3) is met. So, $\mathbf{x}(t)$ is the instantaneously valid dynamic phasor of $x(t)$ for arbitrary $\theta(t)$.

As shown in Fig. 1, applying the dynamic phasor of (1) to RLC circuits in real space results in complex RLC circuits with imaginary impedance in phasor space.

Let us consider the linear time-invariant inductor case first, assuming $m = 1$ from now on for simplicity, as follows:

$$L \dot{\mathbf{i}}_L(t) = \mathbf{v}_L(t) \quad (7a)$$

$$\begin{aligned} \rightarrow L \dot{\mathbf{i}}_L(t) &= L \text{Re} \left[\left\{ \dot{\mathbf{i}}_L(t) + j\dot{\theta}(t) \mathbf{i}_L(t) \right\} e^{j\theta(t)} \right] \\ &= \text{Re} \left\{ \mathbf{v}_L(t) e^{j\theta(t)} \right\} \end{aligned} \quad (7b)$$

$$L \dot{\mathbf{i}}_L(t) + j\dot{\theta}(t) L \mathbf{i}_L(t) \equiv L \overset{\leftrightarrow}{\dot{\mathbf{i}}}_L(t) + jX_L(t) \mathbf{i}_L(t) = \mathbf{v}_L(t). \quad (7c)$$

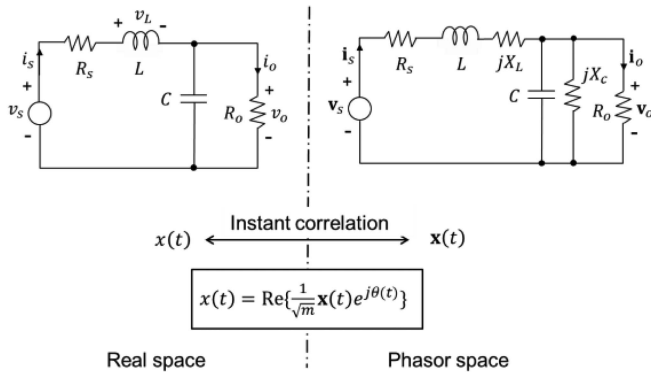
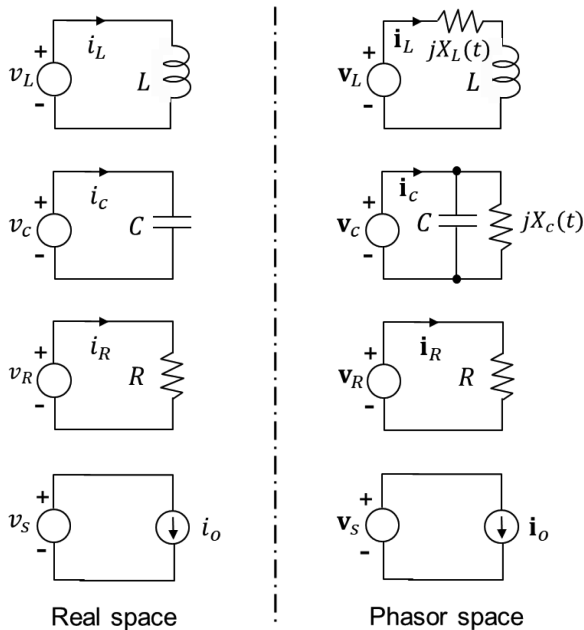


Fig. 1. Proposed instantaneous dynamic phasor in time domain.

Fig. 2. Instantaneous dynamic phasor of LCR circuits and voltage or current sources for arbitrary phase $\theta(t)$.

The equivalence of (7b) and (7c) is proved in the literature [15] for any time-varying $\theta(t)$, which is not a constant value. The phasor transformation for RLC components including inductor is described in more detail in [4], Sec. II-B. Note from (7b) that the time-varying reactance becomes time-invariant only when the phase $\theta(t)$ is linear w.r.t. time t , i.e., $\theta(t) = \omega t$ as follows:

$$X_L(t) = \dot{\theta}(t) L = \omega L \quad (8)$$

which is the well-known reactance of an ac inductor; however, this reactance is valid not only for the static case but also for the dynamic case. The results for (7) are drawn in the circuits of Fig. 2, removing “(t)” term for simplicity, except for the time-varying reactance.

In a very similar fashion, the instantaneous dynamic phasor for a linear time-invariant capacitor becomes as follows:

$$C\dot{v}_c(t) = i_c(t) \quad (9a)$$

$$C\dot{v}_c(t) + j\dot{\theta}(t) C v_c(t) \stackrel{\leftrightarrow}{=} C\dot{v}_c(t) + \frac{v_c(t)}{jX_C(t)} = i_c(t) \quad (9b)$$

$$X_C(t) \equiv -1/\left\{\dot{\theta}(t) C\right\} = -1/(\omega C) \text{ for } \theta(t) = \omega t. \quad (9c)$$

The instantaneous dynamic phasor for a linear time-invariant resistance also becomes as follows:

$$Ri_R(t) = v_R(t) \leftrightarrow Ri_R(t) = v_R(t). \quad (10)$$

The instantaneous dynamic phasor for a voltage and current source is defined from (1), given as follows:

$$v_s(t) = \text{Re}\left\{v_s(t) e^{j\theta(t)}\right\} = \text{Re}\left\{v_s(t) e^{j\omega t}\right\} \text{ for } \theta(t) = \omega t \quad (11a)$$

$$i_o(t) = \text{Re}\left\{i_o(t) e^{j\theta(t)}\right\} = \text{Re}\left\{i_o(t) e^{j\omega t}\right\} \text{ for } \theta(t) = \omega t. \quad (11b)$$

Note from (11) that $v_s(t)$ and $i_o(t)$ would become slowly varying envelopes of $v_s(t)$ and $i_o(t)$, respectively, if $v_s(t)$ and $i_o(t)$ are sinusoidal waveforms of ω . However, this is not the mandatory condition for the instantaneous dynamic phasor of (1). So, the dynamic phasor so far discussed above is valid for arbitrary source and output frequencies which could be different from ω , i.e., $\omega \neq \omega_s \neq \omega_o$.

As a summary, it can be said that the dynamic phasor, as shown in Figs. 1 and 2, instantly relate the real space with the phasor space for arbitrary time-varying phase or arbitrary nonzero frequency. Of course, a practically useful dynamic phasor is only obtained for $\omega = \omega_s = \omega_o$.

B. Reinterpretation of the Generalized Averaging

The original generalized averaging method [5] is retrieved here because there is no change in the principle of the techniques despite the change of names to dynamic phasor now.

The waveform $x(t)$ is expanded on the interval $(t - T, t]$ in a Fourier series representation of the form

$$x(t - T + s) = \sum_{k=-\infty}^{\infty} \langle x \rangle_k(t) e^{jk\omega_s(t-T+s)} \quad (12)$$

where the sum is over all integers k and $\omega_s = 2\pi/T$, $s \in (0, T]$, and $\langle x \rangle_k(t)$ are complex Fourier coefficients as follows:

$$\langle x \rangle_k(t) = \frac{1}{T} \int_0^T x(t - T + s) e^{-jk\omega_s(t-T+s)} ds. \quad (13)$$

Since (13) is an average value over the past time of T , the generalized averaging model needs all the information on $x(t - T + s)$ for $s \in (0, T]$. In other words, we should wait for a period of time T to get the dynamic phasor information.

The time derivative of the k th Fourier coefficient becomes

$$\frac{d}{dt} \langle x \rangle_k(t) = \left\langle \frac{d}{dt} x \right\rangle_k(t) - jk\omega_s \langle x \rangle_k(t). \quad (14)$$

It is interesting that (14) is also valid for a partial averaging case on the interval $s \in (t - \Delta T, t]$, where $0 < \Delta T < T$ as follows:

$$\langle x \rangle_k(t) = \frac{1}{\Delta T} \int_0^{\Delta T} x(t - \Delta T + s) e^{-jk\omega_s(t - \Delta T + s)} ds \quad (15)$$

which is no longer the Fourier coefficient; so, the Fourier series of (12) is not valid for (15). If this partial averaging of (15) is effective, we do not have to wait for a period of time T to get the dynamic phasor information. Note that (14) is also valid for any ΔT , which is arbitrarily large, i.e., $T \leq \Delta T$.

In practice, reasonably enough time is requisite for achieving reliable dynamic phasor information, which could be eventually multiples of T considering periodic switching harmonics. The calculation time T_c for the dynamic phasor, however, it is not necessarily governed by T as identified from the literature, for example, [16] and [17]. Either $T_c \leq T$ or $T_c > T$ is possible according to the signal processing algorithm. Although $T_c = T$ is often preferred due to periodic characteristics of switching converters, it is inherently nothing to do with the validation of (14).

As (14) is applied to an RLC circuit with voltage and current sources in real space, an equivalent circuit in the phasor space can be obtained. The example for an inductor is as follows:

$$\begin{aligned} L \frac{d}{dt} \langle i \rangle_k(t) &= \left\langle L \frac{d}{dt} i \right\rangle_k(t) - jk\omega_s L \langle i \rangle_k(t) \\ &= \langle v \rangle_k(t) - jk\omega_s L \langle i \rangle_k(t) \end{aligned} \quad (16a)$$

$$\rightarrow L \frac{d}{dt} \langle i \rangle_k(t) + jk\omega_s L \langle i \rangle_k(t) = \langle v \rangle_k(t). \quad (16b)$$

Note that (16b) is the same form of (7c) and that the application of the generalized averaging model to other circuits, such as C and R, also has similar forms of (9) and (10) if only $\dot{\theta}(t) = \omega = k\omega_s$.

It should be remarked that even though we can get the dynamic phasor information with (15), there is no way to relate its corresponding (14) with (12) at the moment. In other words, it has been verified that extending the generalized averaging to the partial averaging case is not possible.

C. Comparison of Dynamic Phasors

There are a few differences among the dynamic phasor models: the phasor transformation, the generalized averaging, and the proposed extended dynamic phasor.

As summarized in Table I, one of them is its validity in the time domain. Inherently, the phasor transformation and its extended version proposed here are valid for the instantaneous time domain, but the generalized averaging is not instantaneously valid for.

Different from the single frequency of the phasor transformation, however, multiple switching harmonics can be examined by the generalized averaging model. The extended phasor transformation, however, enables us to use an arbitrary phase angle, which embraces nonperiodic switching cases and multiple harmonics.

TABLE I
COMPARISON OF DYNAMIC PHASOR MODELS

Comparison Issues	Original Phasor Transformation [4]	The Generalized Averaging [5]	Proposed Extended Phasor Transformation
Validity	Instantaneously	Averaged only	Instantaneously
Frequency	Single ($\omega = \omega_s$)	Multiple ($\omega = k\omega_s$)	Arbitrary $\dot{\theta}(t)$
Phase	-	-	Arbitrary $\theta(t)$
Periodicity	Must be periodic	Must be periodic	Need not periodic
Eq. circuit	Available	Not available	Available
Fourier series	Not needed	Requisite	Not needed
Switching converter	Auto transformer	Describing function	Auto transformer
LC resonant circuit	Reduced order possible	No reduced order	Reduced order possible

The phasor transformation and its extended version have several merits over the generalized averaging. Equivalent circuits in the phasor space are always available, including switching converters, which are found to be time-invariant auto-transformers. A serial or parallel LC resonant circuit of the second-order system can be degenerated to the first order for the tuned case and the zeroth order system for the mistuned case.

III. LAPLACED DYNAMIC PHASOR

In the ac power analyses, Laplace domain equivalent circuits are quite useful and highly needed for the system design. For simplicity, the Laplace transformation is applied to the dynamic phasor at a fixed frequency with time-varying amplitude as follows:

$$x(t) = \text{Re} \{ \mathbf{x}(t) e^{j\omega_s t} \}. \quad (17)$$

The term ‘‘Laplaced’’ is adopted in this article as the abbreviation of ‘‘Laplace transform of,’’ which is a quite widely used word in modeling.

A. Laplaced LCR Circuits of Dynamic Phasor

The dynamic phasor equation for a linear time-invariant inductor of (7) under the condition of (8) is examined as follows:

$$L \dot{\mathbf{i}}_L(t) + j\omega L \mathbf{i}_L(t) = \mathbf{v}_L(t). \quad (18)$$

Note that the Laplace transformation for the general instantaneous dynamic phasor of (7) does not give us of simple and conventional linear form of results. Since (18) is of linear time-invariant form, the Laplace transform can be applied to this equation, which is as follows:

$$(s + j\omega) L \mathbf{i}_L(s) = \mathbf{v}_L(s) \leftrightarrow \mathbf{i}_L(s) = \frac{\mathbf{v}_L(s)}{(s + j\omega) L}. \quad (19)$$

Bold characters are not used for the Laplace variables because it is a convention. In a similar fashion, the Laplace transformed capacitor and resistor of (9) and (10) under (8) become

$$(s + j\omega) C \mathbf{V}_c(s) = \mathbf{I}_c(s) \leftrightarrow \mathbf{V}_c(s) = \frac{\mathbf{I}_c(s)}{(s + j\omega) C}. \quad (20a)$$

$$R \mathbf{I}_R(s) = \mathbf{V}_R(s). \quad (20b)$$

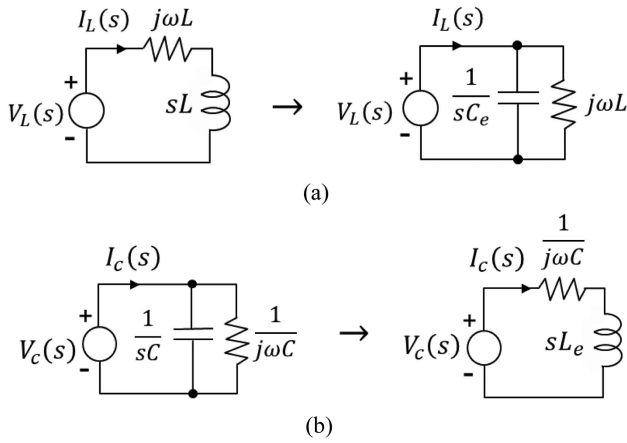


Fig. 3. Approximated equivalent circuits (right side) for (a) Laplace inductor and (b) capacitor in the phasor space.

	Real space	Phasor space
Time domain	$v_s(t) \rightarrow G_v(t) \rightarrow v_o(t)$ $v_o(t) = G_v(t) * v_s(t)$	$\mathbf{v}_s(t) \rightarrow \mathbf{G}_v(t) \rightarrow \mathbf{v}_o(t)$ $\mathbf{v}_o(t) = \mathbf{G}_v(t) * \mathbf{v}_s(t)$
Laplace domain	$V_s(s) \rightarrow G_v(s) \rightarrow V_o(s)$ $V_o(s) = G_v(s) \cdot V_s(s)$	$\mathbf{V}_s(s) \rightarrow \mathbf{G}_v(s) \rightarrow \mathbf{V}_o(s)$ $\mathbf{V}_o(s) = \mathbf{G}_v(s) \cdot \mathbf{V}_s(s)$ $= G_v(s + j\omega_s) \cdot \mathbf{V}_s(s)$

where * denotes (linear) convolution.

Fig. 4. System gains in the real space (left) and phasor space (right), where the frequency shift is found.

It is noteworthy that (19) and (20a) can be approximated for slow dynamics, respectively, as follows:

$$\begin{aligned}
 I_L(s) &= \frac{V_L(s)}{j\omega L \left(1 + \frac{s}{j\omega}\right)} \cong \frac{V_L(s)}{j\omega L} \left(1 - \frac{s}{j\omega}\right) \\
 &= V_L(s) \left(\frac{1}{j\omega L} + \frac{s}{\omega^2 L}\right) \\
 &\cong \frac{V_L(s)}{j\omega L} + sC_e V_L(s). \quad \because C_e = \frac{1}{\omega^2 L}
 \end{aligned} \quad (21a)$$

$$\begin{aligned}
 V_C(s) &= \frac{I_C(s)}{j\omega C \left(1 + s/j\omega\right)} \cong \frac{I_C(s)}{j\omega C} \left(1 - \frac{s}{j\omega}\right) \\
 &= I_C(s) \left(\frac{1}{j\omega C} + \frac{s}{\omega^2 C}\right) \\
 &\cong \frac{I_C(s)}{j\omega C} + sL_e I_C(s) \quad \because L_e = \frac{1}{\omega^2 C}
 \end{aligned} \quad (21b)$$

for $|s| \ll \omega$. (21c)

From (21a) and (21b), it is identified that the Laplace transformed inductor (capacitor) in the phasor domain can be approximated to an imaginary resistor in parallel (series) with an equivalent capacitor (inductor), as shown in Fig. 3. Interestingly, the approximated equivalent circuit for an inductor resembles

the capacitor circuit and vice versa. Note that this equivalence is valid only for the condition of (21c), which is found for specific LC resonant tank circuits only [4], but is now proved to be valid for any ac circuits in general.

B. Laplaced Sources of Dynamic Phasor

In case the source voltage or current of a linear time-invariant ac power system is sinusoid at a fixed frequency and phase with time-varying amplitude, the Laplace transform can be applied to the system. For example, the source voltage $v_s(t)$ in Fig. 1 can be represented as the product of an envelope function $v_e(t)$ of real value and a sinusoid with a fixed frequency and phase ϕ_s as follows:

$$v_s(t) \equiv v_e(t) \cos(\omega_s t + \phi_s) = \text{Re} \{v_e(t) e^{j\omega_s t + j\phi_s}\}. \quad (22)$$

The dynamic phasor of (22) is found for $m = 1$, for simplicity without the loss of generality, and the fixed frequency of ω_s from (1) as follows:

$$v_s(t) = \text{Re} \{\mathbf{v}_s(t) e^{j\omega_s t}\}. \quad (23)$$

Comparing (23) with (22), the voltage source of the dynamic phasor is deduced as follows:

$$\mathbf{v}_s(t) = v_e(t) e^{j\phi_s}. \quad (24)$$

The transfer function of the real space circuit at the left side of Fig. 1 is canonically obtained as follows:

$$G_v(s) \equiv \frac{V_o(s)}{V_s(s)} = \frac{R_o}{(R_s + sL)(1 + sCR_o) + R_o}. \quad (25)$$

Applying the Laplace transform to (22) results in the following:

$$\begin{aligned}
 V_s(s) &= \mathcal{L} \left\{ v_e(t) \frac{e^{j\omega_s t + j\phi_s} + e^{-j\omega_s t - j\phi_s}}{2} \right\} \\
 &= \frac{V_e(s - j\omega_s) e^{j\phi_s} + V_e(s + j\omega_s) e^{-j\phi_s}}{2} \\
 &= \frac{\mathbf{V}_s(s - j\omega_s) + \mathbf{V}_s^*(s + j\omega_s)}{2}.
 \end{aligned} \quad (26)$$

Because (23) is the same form of the dynamic phasor of (17), any variables $x(t)$ and $\mathbf{x}(t)$ in the time domain is Laplace transformed as follows:

$$\mathbf{X}(s) = \frac{\mathbf{X}(s - j\omega_s) + \mathbf{X}^*(s + j\omega_s)}{2}. \quad (27)$$

Note from (26) that the Laplace transform of (24) of the following is used, where the bold character is used to distinguish the Laplaced phasor space variable from the real space variable.

$$\mathbf{V}_s(s) = V_e(s) e^{j\phi_s}. \quad (28)$$

Then, the Laplaced output voltage in real space can be determined from (25) and (26) as the linear sum of the well-known positive and negative sequence phasors as follows:

$$\begin{aligned}
 V_o(s) &= G_v(s) V_s(s) \\
 &= G_v(s) \frac{\mathbf{V}_s(s - j\omega_s) + \mathbf{V}_s^*(s + j\omega_s)}{2}.
 \end{aligned} \quad (29)$$

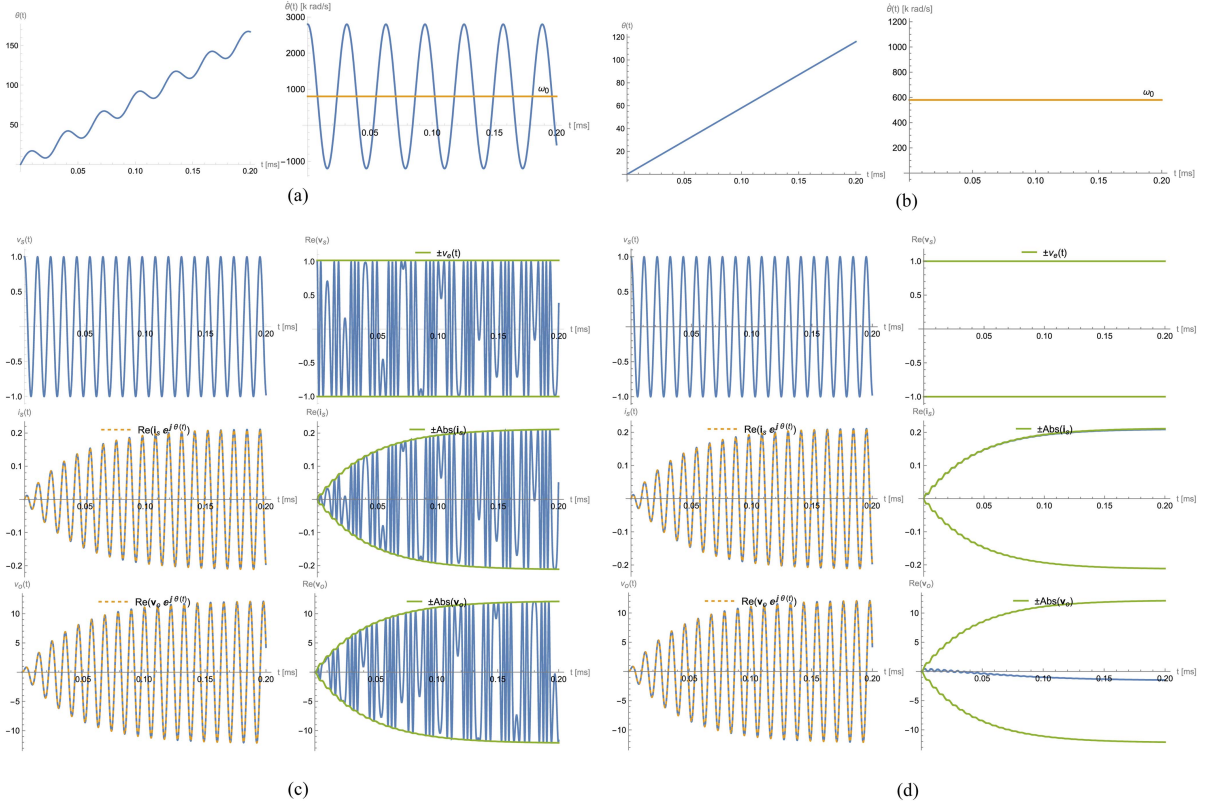


Fig. 5. Simulation of the proposed instantaneous dynamic phasor (left) and generalized averaging (right) for the left and right circuits of Fig. 1 by Mathematica at $\omega_s = 580$ k rad/s. (a) $\theta(t) = \omega_0 t + \alpha \sin \omega_1 t$ (left), and its angular frequency (right). (b) $\theta(t) = \omega_0 t$ (left), and its angular frequency (right). (c) $v_s(t)$, $i_s(t)$, and $v_o(t)$ in real space compared with dynamic phasor (dotted yellow) (left), and \mathbf{v}_s , \mathbf{i}_s , and \mathbf{v}_o in phasor space (right). (d) $v_s(t)$, $i_s(t)$, and $v_o(t)$ in real space compared with dynamic phasor (dotted yellow) (left), and \mathbf{v}_s , \mathbf{i}_s , \mathbf{v}_o in phasor space (right).

Dynamic phasor and its Laplace transform of the output voltage $v_o(t)$ are found from (17) assuming zero initial conditions of the system as follows:

$$v_o(t) = \text{Re} \{ \mathbf{v}_o(t) e^{j\omega_s t} \} \quad (30a)$$

$$\begin{aligned} \therefore V_o(s) &= \mathcal{L} [\text{Re} \{ \mathbf{v}_o(t) e^{j\omega_s t} \}] = \text{Re} [\mathcal{L} \{ \mathbf{v}_o(t) e^{j\omega_s t} \}] \\ &= \text{Re} [\mathbf{V}_o(s - j\omega_s)] = \frac{\mathbf{V}_o(s - j\omega_s) + \mathbf{V}_o^*(s + j\omega_s)}{2} \end{aligned} \quad (30b)$$

Applying (30b) to (29) results in the following equation.

$$\begin{aligned} &\mathbf{V}_o(s - j\omega_s) + \mathbf{V}_o^*(s + j\omega_s) \\ &= G_v(s) \{ \mathbf{V}_s(s - j\omega_s) + \mathbf{V}_s^*(s + j\omega_s) \} \end{aligned} \quad (31)$$

which holds for any s ; therefore, replacing s with $s + j\omega_s$ results in the following frequency-shifted form:

$$\begin{aligned} &\mathbf{V}_o(s) + \mathbf{V}_o^*(s + 2j\omega_s) \\ &= G_v(s + j\omega_s) \{ \mathbf{V}_s(s) + \mathbf{V}_s^*(s + 2j\omega_s) \} \end{aligned} \quad (32)$$

Equation (32) can be decomposed into the following two equations:

$$\mathbf{V}_o(s) = G_v(s + j\omega_s) \mathbf{V}_s(s) \quad (33a)$$

$$\mathbf{V}_o^*(s + 2j\omega_s) = G_v(s + j\omega_s) \mathbf{V}_s^*(s + 2j\omega_s) \quad (33b)$$

Equation (33b) can be further simplified by replacing s with $s - 2j\omega_s$ as follows:

$$\mathbf{V}_o^*(s) = G_v(s - j\omega_s) \mathbf{V}_s^*(s). \quad (33c)$$

Note that (33c) is just the complex conjugate of (33a). Therefore, (33b) and (33c) are simply a degenerated form of (33a).

As shown in Fig. 4, the transfer function of the phasor space system is found to be a frequency shift form of the original one of the real space as follows:

$$\mathbf{G}_v(s) \equiv \frac{\mathbf{V}_o(s)}{\mathbf{V}_s(s)} = G_v(s + j\omega_s). \quad (34)$$

For the proposed example circuit of (25), the system gain in the phasor space of (34) is calculated as follows:

$$\mathbf{G}_v(s) = \frac{R_o}{\{R_s + (s + j\omega_s)L\} \{1 + (s + j\omega_s)CR_o\} + R_o}. \quad (35)$$

Note that (35) is exactly the same as the circuit transfer function of the right part in Fig. 1. As shown in Fig. 4, the envelope behavior, instead of the real-time sinusoid waveform, is directly obtained from the system gain of the phasor space.

IV. SIMULATION FOR INSTANTANEOUS DYNAMIC PHASOR

The proposed extended phasor transformation, as the instantaneous dynamic phasor, is verified by simulation here. For

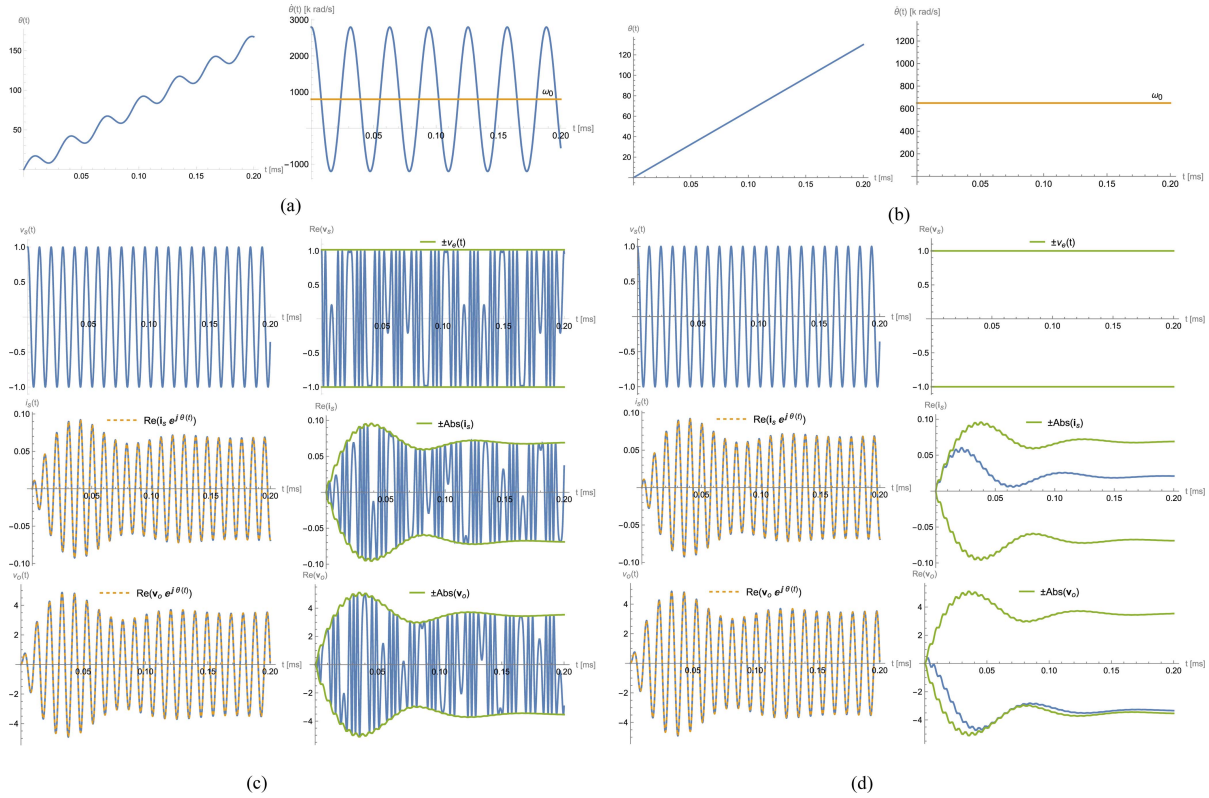


Fig. 6. Simulation of the proposed instantaneous dynamic phasor (left) and generalized averaging (right) for the left and right circuits of Fig. 1 by Mathematica at $\omega_s = 650$ krad/s. (a) $\theta(t) = \omega_0 t + \alpha \sin \omega_1 t$ (left), and its angular frequency (right). (b) $\theta(t) = \omega_0 t$ (left), and its angular frequency (right). (c) $v_s(t)$, $i_s(t)$, and $v_o(t)$ in real space compared with the dynamic phasor (dotted yellow) (left), and \mathbf{v}_s , \mathbf{i}_s , and \mathbf{v}_o in phasor space (right). (d) $v_s(t)$, $i_s(t)$, and $v_o(t)$ in real space compared with the dynamic phasor (dotted yellow) (left), and \mathbf{v}_s , \mathbf{i}_s , and \mathbf{v}_o in phasor space (right).

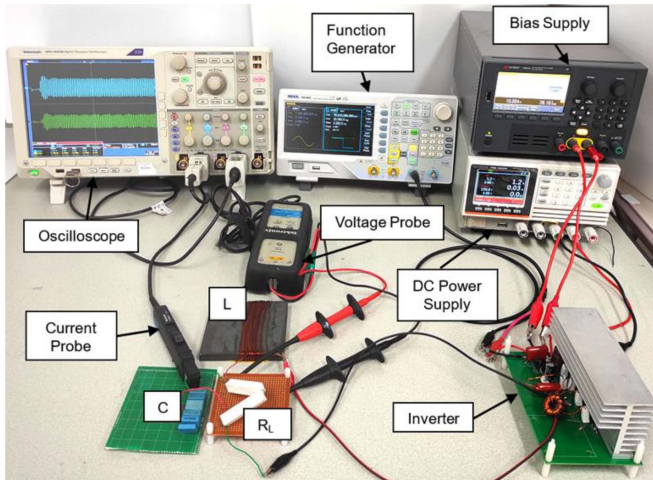


Fig. 7. Experiment kit for the circuit of Fig. 1.

simplicity and showing practical feasibility in a real worthy application in the power electronic field, we have implemented our proposed theory on an RLC circuit. The extended phasor transformation of (1) is applied to an example circuit of an RLC resonant circuit of Fig. 1. The phasor is assumed to be (2). Then, the time-varying reactance for L and C can be determined from

(8) and (9c) as follows:

$$X_L(t) \equiv \dot{\theta}(t) L = (\omega_0 + \alpha \omega_1 \cos \omega_1 t) L \quad (36a)$$

$$X_C(t) \equiv -\frac{1}{\dot{\theta}(t) C} = -\frac{1}{\{\omega_0 + \alpha \omega_1 \cos \omega_1 t\} C}. \quad (36b)$$

The RLC circuit in the phasor space of Fig. 1 is linear time-varying and can be represented as a state equation as follows:

$$L \dot{\mathbf{i}}_s = \mathbf{v}_s - \{R_s + jX_L(t)\} \mathbf{i}_s - \mathbf{v}_o \quad (37a)$$

$$C \dot{\mathbf{v}}_o = \mathbf{i}_s - \mathbf{v}_o/R_o - \mathbf{v}_o/jX_C(t). \quad (37b)$$

Given the source voltage of (22), its dynamic phasor for the FM signal of (2) becomes the following:

$$v_s(t) = \text{Re} \{ v_e(t) e^{j\omega_s t + j\phi_s} \} \equiv \text{Re} \{ \mathbf{v}_s e^{j\theta(t)} \}. \quad (38a)$$

$$\begin{aligned} \therefore \mathbf{v}_s &= v_e(t) e^{j\omega_s t + j\phi_s - j\theta(t)} \\ &= v_e(t) e^{j(\omega_s t + \phi_s - \omega_0 t - \alpha \sin \omega_1 t)}. \end{aligned} \quad (38b)$$

The state equation (37) using (38) is simulated by the Wolfram Mathematica (Ver. 14.1) [21], [22] for the parameters of Table II. As shown in Figs. 5 and 6, the transient responses of real space and the phasor space circuits are obtained assuming zero initial values. As shown in Figs. 5(a) and 6(a), the angular frequency of

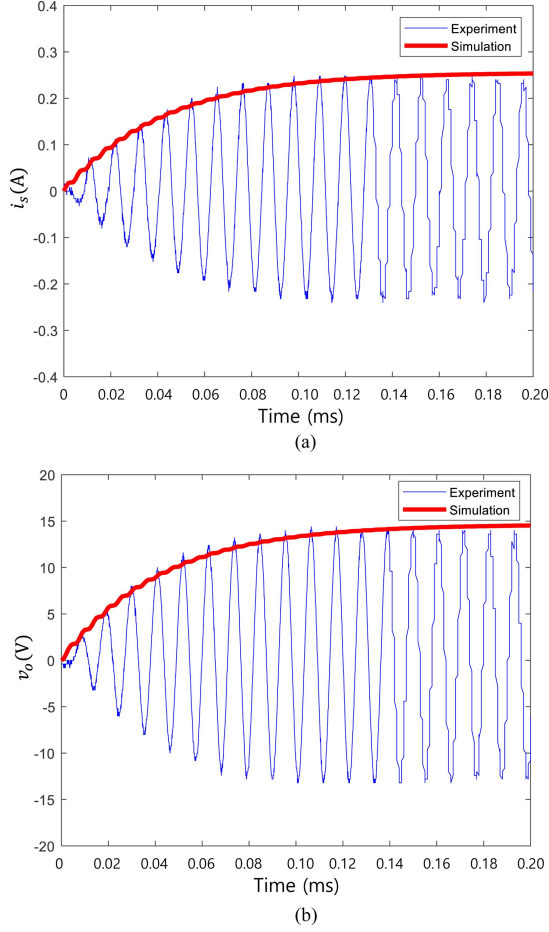


Fig. 8. Simulation and experimental waveforms for the circuit of Fig. 7. (a) $i_s(t)$. (b) $v_o(t)$ at $\omega_s = 580$ krad/s.

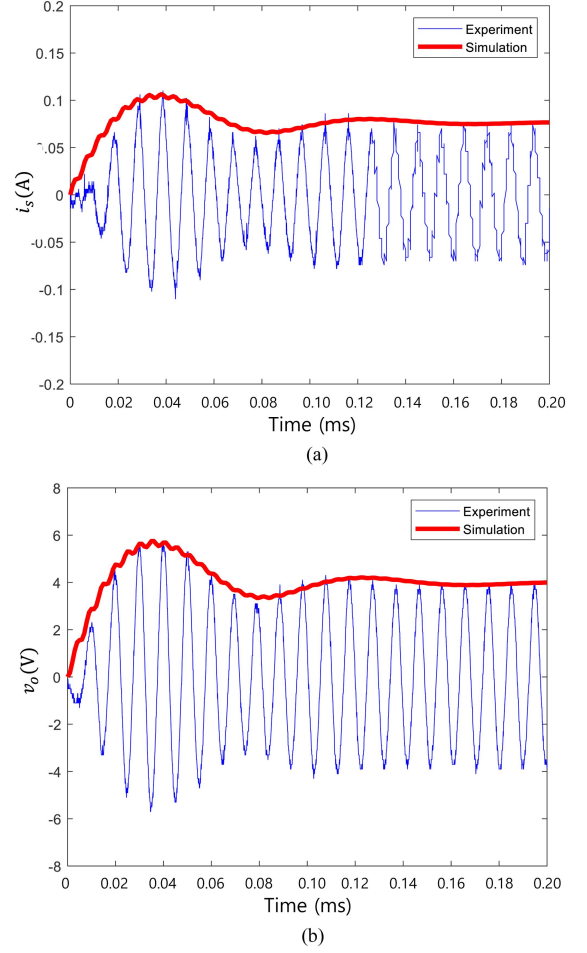


Fig. 9. Simulation and experimental waveforms for the circuit of Fig. 7. (a) $i_s(t)$. (b) $v_o(t)$ at $\omega_s = 650$ krad/s.

TABLE II
CIRCUIT PARAMETERS FOR SIMULATION AND EXPERIMENTS

Parameters	Values
ω_s	580 and 650 k rad/s
ω_0	800 k rad/s
ω_1	200 k rad/s
α	10 rad
L	100.04 μ H
C	30.07 nF
R_s	3.0 Ω
R_o	2.00 k Ω

the dynamic phasor is severely time-varying and quite different from the constant source voltage angular frequency. With a step function of $v_e(t)$, i_s and v_o in real space perfectly overlap with the real part of \mathbf{i}_s and \mathbf{v}_o as in (1), which are shown in dotted yellow line; so, it is indistinguishable each other, as shown in the left part of Figs. 5(c) and 6(c). The phasor space variables are severely modulated and quite different from the real space ones; however, the envelopes of them, i.e., the absolute values, depict the system response, as shown in the right part of Figs. 5(c) and 6(c). The phasor space variables would simply show the envelope of real space variables if it were the conventional dynamic phasor of

$\theta(t) = \omega_s t$, which is a special case of $\alpha = 0$, that becomes a generalized averaging case, as shown in Figs. 5(b) and (d) and 6(b) and (d).

Note that the envelope of the output voltage for $\theta(t) = \omega_s t$ can be analyzed from (35) for (24) and (28) [21], [22].

$$\mathbf{V}_o(s) = \mathbf{G}_v(s) \mathbf{V}_s(s) = \mathbf{G}_v(s) V_e(s) e^{j\phi_s} \quad (39a)$$

$$\therefore \mathbf{v}_o(t) = \mathcal{L}^{-1}\{\mathbf{V}_o(s)\} \equiv K \{1 - p_1(t) p_2(t)\} \quad (39b)$$

$$\begin{aligned} \therefore K &= \frac{R_o e^{j\phi_s}}{R_o + R_s - LCR_o\omega_s^2 + j\omega_s(L + CR_oR_s)} \\ V_e(s) &= \frac{1}{s}, p_1(t) = e^{-\frac{t}{\tau}} \left(\frac{1}{CR_o} + \frac{R_s}{L} \right) - j\omega_s t, \phi_s = 0 \\ p_2(t) &= 1 - \left\{ \cos\omega_p t + \left(\frac{1}{2CR_o} + \frac{R_s}{2L} + j\omega_s \right) \frac{\sin\omega_p t}{\omega_p} \right\}, \\ \omega_p &= \frac{\sqrt{4LCR_o^2 - (L - CR_oR_s)^2}}{2LCR_o}. \end{aligned} \quad (39c)$$

As can be seen from (39b), the beat frequency observed in the envelopes of Figs. 5(c) and 6(c) are generated from the product term of $p_1(t)p_2(t)$, where ω_s and ω_p are included in $p_1(t)$ and

$p_2(t)$, respectively. It is verified by the Mathematica simulation that (39) exactly matches the envelopes of Figs. 5(c) and 6(c).

It is identified through extensive simulation that there is no mismatch at all between the real space and phasor space circuits' waveforms for every possible change in the eight variables of Table II. Therefore, it can be said that the dynamic phasor instantly correlates the real space with the phasor space successfully, regardless of the phase angle $\theta(t)$ of (2).

V. EXPERIMENTAL VERIFICATIONS FOR DYNAMIC PHASOR

The *RLC* circuit of Fig. 1 and a full bridge inverter are implemented with the parameters in Table II, as shown in Fig. 7. Note that R_s includes the overall resistance of the circuit elements, i.e., inverter internal resistance and *LC* tank resistance. The time domain phasor space response of (39b) for a step change in the envelope of the source voltage is experimentally verified at $\omega_s = 580$ and 650 krad/s, as shown in Figs. 8 and 9, respectively. The measured waveforms of Figs. 8 and 9 are also well matched to the simulated envelopes of Figs. 5 and 6. It is observed that there is a percentage error of less than 3% in the current $i_s(t)$ and voltage $v_o(t)$ magnitudes between the simulation and experiments.

VI. CONCLUSION

The proposed instantaneous dynamic phasor is compared with the generalized averaging and fully verified by simulation and experiments. The dynamic phasor is instantly valid for any time and is not necessarily related to the period of the voltage or current source of ac power systems. The instantaneous dynamic phasor is valid for an arbitrary and even time-varying frequency, which is not necessarily the same as the source frequency. The transfer function of the phasor space system is found to be a frequency shift form of the original one of the real space system for the fixed frequency dynamic phasor.

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