

Low SNR FreeDV Mode

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1 Glossary

Acronym	Explanation
AWGN	Additive White Gaussian Noise - a communications channel with flat frequency response and additive noise
CP	Cyclic Prefix
FEC	Forward Error Correction
LEO	Low earth orbit satellite channel, AWGN with large freq offset and Doppler shift (high rate of change of freq offset)
GEO	Geosynchronous satellite channel, AWGN but high phase noise and large freq offset
PTT	Push To Talk - voice communications where only one person is transmitting at any one time. Common in two way radio but not mobile telephones
MPP	Multipath Poor channel, 1 Hz Doppler, 2ms delay spread, typical for US and Australian interstate propagation
MPD	Multipath Disturbed channel, 2 Hz Doppler, 4ms delay spread, typical for UK Winter NVIS propagation

Table 1: Glossary of Acronyms

2 Introduction

After 10 years development and on air experience with various FreeDV waveforms, we would like to develop a new waveform that outperforms and replaces a variety of existing modes such as 700C/D/E and 1600. Requirements include [1]:

¹Can be expressed as a linear ratio E_b/N_0 or $10\log_{10}(E_b/N_0)$ dB

Symbol	Explanation	Units
B	Noise bandwidth	Hz
E_b/N_0	Energy per bit on spectral noise density	dimensionless, dB ¹
N_s	Spacing between pilots (pilot insertion rate)	-
R_b	Bit rate	Bits/second
R_s	Symbol rate	symbols/second
T_s	Symbol period	seconds
SNR	Signal to Noise Ratio	dB
S	Signal Power	Watts
N	Noise Power	Watts

Table 2: Glossary of Symbols

1. Better performance than SSB at 0dB SNR on MPP and MPD channels.
2. A single mode that can handle MPP, MPD, GEO (e.g. QO-100), and replace several existing FreeDV modes, simplifying the end user experience.
3. For compliance with Export Control regulations, the minimum speech codec bit rate is 700 bit/s.

It is acceptable for performance to gradually decrease as the multipath channel quality declines, but we would like the decline to be gradual, e.g. a few dB more power for operation on MPD versus MPP.

This document explores ways we can improve the existing OFDM modem waveforms in order to meet these requirements.

3 Modem Performance Model

In this section we will develop a theoretical model to help us explore performance limits. For practical PTT voice systems algorithmic delay is limited to a few 100ms, which limits the FEC codeword size and hence the performance of the code. For PSK channels a threshold $E_b/N_0 = 2$ dB and a code rate $R = 0.5$ is typical, where E_b/N_0 is the energy per payload data bit (coded E_b/N_0). The lowest (threshold) SNR for a viable voice link is given by:

$$\frac{S}{N} = \frac{E_b R_b}{N_0 B} \quad (1)$$

$$SNR = 10 \log_{10} \left(\frac{E_b}{N_0} \right) + 10 \log_{10} \left(\frac{R_b}{B} \right) \quad [\text{dB}]$$

where R_b is the payload data bit rate, and B is the bandwidth in which we measure SNR. Given $R_b = 700$ and $B = 3000$ we have:

$$SNR = 2 + 10 \log_{10}(700/3000) \quad (2)$$

$$= -4.3 \text{ dB}$$

This is ideal performance for an AWGN channel. In practice we must allocate some power to symbols used for synchronisation, such as pilot symbols used for frequency and phase estimation, or unique word bits used for frame synchronisation. Synchronisation algorithms often struggle at low SNRs, introducing additional "implementation" losses.

Performance on multipath channels is significantly worse, in our use cases typically 5 dB. On these channels, we may allocate some carrier power to deal with intersymbol interference (for example a cyclic prefix in OFDM modems).

A more complete model is:

$$SNR = 10\log_{10} \left(\frac{E_b}{N_0} \right) + 10\log_{10} \left(\frac{R_b}{B} \right) + L_p + L_{il} + L_{cp} \quad (3)$$

where L_p is the loss from power allocated to pilot symbols, L_{il} is the real world implementation loss, and L_{cp} is the loss in SNR due to the power allocated to the cyclic prefix.

TODO: Discuss Available bandwidth. 2000 Hz, using QPSK we can get 4000 bits/s. Less overheads (which can be expressed as SNR or bandwidth reduction?). We have 700 bits/s source code or 1400 bits/s with rate 0.5 FEC.

3.1 Pilot symbol overhead

In this section we explore the effect of inserting pilot symbols on the threshold SNR (1). Consider a sequence of $N_s - 1$ PSK data symbols that carry the modulated FEC codeword bits (e.g. data and parity bits) over the channel. We denote this sequence a *frame*. The frame of $N_s - 1$ symbols has a period of $T_f = (N_p - 1)T_s$ seconds, where T_s is the period of each symbol. We wish to insert a single pilot symbol after the data symbols, creating a new frame N_s symbols long, with period $T'_f = N_p T_s$. To maintain the same payload data rate:

$$\begin{aligned} T_f &= T'_f \\ (N_s - 1)T_s &= N_s T_s \\ R'_s &= R_s \frac{N_s}{N_s - 1} \end{aligned} \quad (4)$$

where the symbol rate $R_s = 1/T_s$. Expressing S/N (1) in terms of E_s and R_s :

$$\begin{aligned} \frac{S}{N} &= \frac{E_s R_s}{N_0 B} \\ \frac{S'}{N} &= \frac{E_s R'_s}{N_0 B} \\ &= \frac{E_b R_s N_s}{N_0 B (N_s - 1)} \\ \frac{S'/N}{S/N} &= \frac{N_s}{N_s - 1} \end{aligned} \quad (5)$$

Thus when we insert pilots, the threshold S/N increases by a factor of $N_s/(N_s - 1)$. Expressed in dB:

$$\begin{aligned} 10\log_{10}\left(\frac{S'}{N}\right) &= 10\log_{10}\left(\frac{S}{N}\right) + 10\log_{10}\left(\frac{N_s}{N_s - 1}\right) \\ SNR' &= SNR + 10\log_{10}\left(\frac{N_s}{N_s - 1}\right) \\ SNR' &= SNR + L_p \quad [\text{dB}] \end{aligned} \tag{6}$$

where L_p can be considered the pilot symbol *loss* - the SNR degradation from the ideal performance (1) due to the insertion of pilot symbols. For example FreeDV 700D uses a pilot insertion rate of $N_s = 8$ results in $L_p = 10\log_{10}(8/7) = 0.58$ dB, thus we need 0.58 dB more SNR to achieve the threshold SNR for the voice link.

3.2 Cyclic Prefix Overhead

TODO- fix, should just be one factor of $1 - T_{cp}/T_s$ I think.

Now we consider the SNR overhead for the Cycle Prefix (CP) used in OFDM modems to cope with delay spread on multipath channels. To achieve our payload data rate (e.g. 700 bits/s), we send symbols D across the channel at a constant symbol rate R_s , or one symbol every $T = T_s$ seconds. To cope with delay spread, we construct a composite symbol by pre-pending a Cyclic Prefix (CP) T_{cp} seconds in duration to a new symbol D' of T'_s seconds in duration. D and D' contain the same PSK symbol, and convey the same information over the channel. The new composite symbol is now $T' = T_{cp} + T'_s$ seconds long. The CP contains no additional information, it is just an extension of the single symbol D' . Thus we still send one symbol of data over the channel every T' seconds. To maintain the payload data rate over the channel, we must send the new composite symbol at the same rate as the original symbol:

$$\begin{aligned} T &= T' \\ T_s &= T_{cp} + T'_s \\ R'_s &= \frac{R_s}{1 - T_{cp}/T_s} \end{aligned} \tag{7}$$

It can be observed that $R'_s > R_s$, to account for the portion of the composite symbol allocated to the CP. For example with $R_s = 700$, $T_s = 0.02$, $T_{cp} = 0.002$, $R'_s = 700/(1 - 0.002/0.02) = 777.78$ symbols/second.

For the composite signal, the transmitter power S is spread between the CP and D' :

$$S = \frac{T_{cp}}{T_s} S + \left(1 - \frac{T_{cp}}{T_s}\right) S \tag{8}$$

Only the RH term contributes to the demodulation of D' :

$$\begin{aligned}
\frac{S(1 - T_{cp}/T_s)}{N} &= \frac{E_s R'_s}{N_0 B} \\
\frac{S}{N} &= \frac{E_s R'_s}{N_0 B} \frac{1}{(1 - T_{cp}/T_s)} \\
&= \frac{E_s R_s}{N_0 B} \frac{1}{(1 - T_{cp}/T_s)^2} \\
SNR &= 10 \log_{10} \left(\frac{E_s R_s}{N_0 B} \right) - 20 \log_{10} (1 - T_{cp}/T_s) \\
&= 10 \log_{10} \left(\frac{E_s R_s}{N_0 B} \right) + L_{cp} \quad [\text{dB}]
\end{aligned} \tag{9}$$

Thus to close the link with the composite symbol the S/N must be increased by a factor of $1/(1 - T_s/T_{cp})^2$ compared to our ideal modem. This accounts for the energy allocated to the CP, and the shorter period T'_s of the symbol D' . The squared term suggest SNR is quite sensitive to increasing T_{cp} , which is necessary to handle fast fading, high delay spread channels such as MPD. For example FreeDV 700E has $T_s = 0.02$, $T_{cp} = 0.006$, giving $L_{cp} = -20 \log_{10} (1 - 0.006/0.02) = 3.1 \text{dB}$.

3.3 Waveform Improvements

Try low risk approaches to start with, then iterate. To simulate performance with voice codec, use PER=0.1, BER=0.01 voice codec threshold for modem tests alone.

3.4 Equalisation

1. Pilot symbols are used to estimate channel.
2. Phase and amplitude shifts due to the channel impulse response. For example consider two path model, has time varying complex coeffs and delay.
3. Consider Two path model, comprised of two time varying complex coefficients, with bandwidth (-20dB) of $B = 1 \text{ Hz}$ (MPP). The model is considered stationary over one symbol.
4. We should be able to reconstruct a 1Hz bandwidth signal at 1 Hz sample rate, which suggests a low pilot insertion rate. The other factor is how channel estimate noise.
5. Each coefficient h_n is a complex random variable with bandwidth B . Consider the channel model applied to steady state symbol (or a time varying PSK signal after ISI has settled). Two terms of bandwidth B add linearly, so by linearity the result also has bandwidth B . The sum is a random

modulation of bandwidth B about on the symbol centre frequency. The Doppler bandwidth B therefore defines the bandwidth required for equalisation, independent of delay spread. One caveat - if B an appreciable fraction of R_s the DFT orthogonality may break down to some extent as energy falls into adjacent DFT bins.

6. 700D samples pilots at $1/(N_p * T_s) = 6.25\text{Hz}$, which should be adequate for our target channels. This is an acceptably low L_{ps} SNR overhead.
7. Move from block average to 2D interpolator with bandwidth of (say 6Hz). Simulation, show it can do a better job than block estimator.
8. Benefit - wide Doppler bandwidth, small pilot overhead, low noise channel estimator

3.5 Multipath

$n=2$ diversity to handle multipath. Say 3dB gain on MPP/MPD. Research combining techniques. Risks are copies will have half power so estimators make not work as well.

3.6 FEC

If we use diversity, I am not sure how much FEC we can also use, as we may run out of bandwidth. Alternative is MAP techniques or some combination of MAP and FEC.

3.7 Delay Spread (ISI)

1. We need a CP long enough to handle MPD (4ms plus guard)
2. Try longer T_s which will mean less overhead. However this implies lower R_s which may be impacted by frequency spreading effect of Doppler.
3. Measure implementation loss or EVM against ISI, we might be able to get away with some ISI, it is acceptable to have performance drop off for MPD, but it needs to be gradual rather than breaking.
4. 700C had just 13ms symbols but dealt with ISI pretty well - this might be worth exploring.

4 Unorganised Notes

TODO:

- Can we include PAPR into model? Can we have different trajectories for QPSK symbols around unit circle that reduce PAPR? No I don't think that helps when multiple carriers are added together. ECSSB techniques may be useful.

- Expression for Fading channels, block error rate, why 2020 is a lemon.
- Table of FreeDV waveforms and values, plugged into formula, effect of increasing pilot symbol rate.
- Check performance of a few codes against 2dB figure above.
- Where we can gain, diversity, PAPR reduction, reduced overheads for fast fading and ISI (discuss)
- Wades MAP techniques (ref). This has a lot of promise, need an effective way to simulate and establish benefit with a modest amount of work. Without a rate 0.5 code this would free up a lot of bandwidth to deal with ISI better, e.g. we could have large gaps between symbols. Or use parallel tone modem to reduce effects of ISI. A high rate code on top of this may be useful option (if it can converge). Can we combine MAP with extra bits? Index optimisation also a simple approach.

References

- [1] David Rowe. FreeDV-020 WP4000 Low SNR Mode.