

Analog Transmission of Vocoder Features over Radio Channels

March 9, 2024

Given a vector of vocoder features \mathbf{f} , use an autoencoder E to map them to a dimension d latent vector \mathbf{z} where d is even. Unlike digital modulation, each element z_i of \mathbf{z} is continuously valued and not constrained to a discrete set of points. For bandwidth efficient transmission over the channel the elements of \mathbf{z} are mapped to $d/2$ complex symbols \mathbf{q} . Compared to classical digital modulation, the elements of \mathbf{z} can be considered BPSK symbols (continuously valued, analog bits), and the elements of \mathbf{q} analog QPSK symbols.

Our goal is to determine if reasonable speech quality can be obtained over a channel of bandwidth $B < 3000$ Hz and SNR (measured in $B = 3000$ Hz) of between 0 and 6dB, roughly the lower limit of Single Side Band (SSB) - a common power and bandwidth efficient form of analog radio communication.

1 Simulation of AWGN Channels

The autoencoder output \mathbf{z} is updated every $T_z = 1/R_z$ seconds, giving a BPSK symbol rate of:

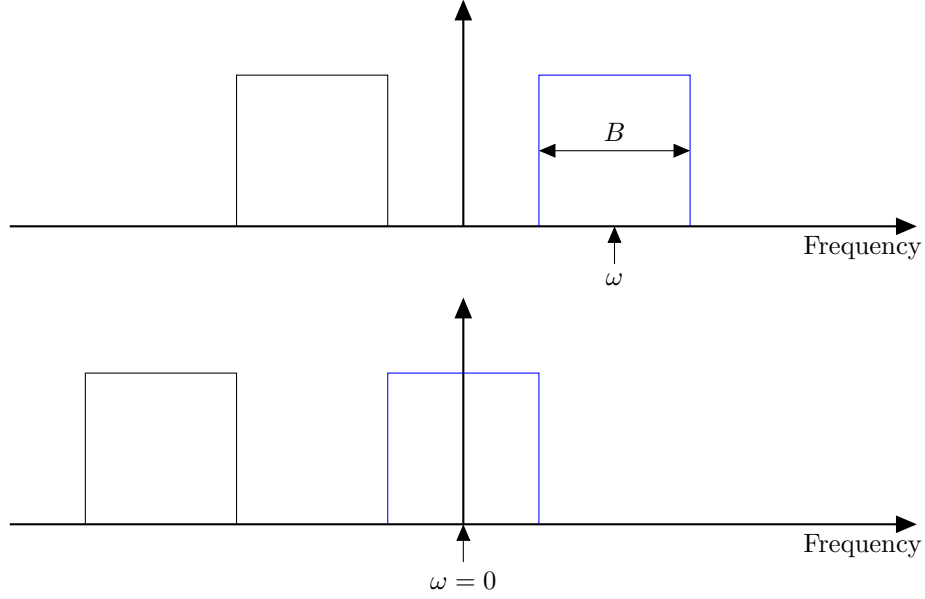
$$R_b = d/T_z \tag{1}$$

For example with $T_z = 0.04$, $d = 80$, $R_b = 2000$ symbols/s. The QPSK symbol rate is given by:

$$R_q = \frac{d}{2T_z} \tag{2}$$

For example with $T_z = 0.04$, $d = 80$, $R_q = 1000$ symbols/s.

Figure 1: Real sampled off-air signal. We are interested in the blue bandpass interval of bandwidth B , which is single sided and hence complex valued. After shifting to baseband, it's power is unchanged, and it remains complex valued.



We wish to simulate an AWGN channel with a user-defined E_b/N_0 , where E_b is the energy of each BPSK symbol, and N_0 is the noise power per unit bandwidth. Consider a real valued signal sampled off air (Figure 1). We will follow convention and define signal and noise power in the “single sided” bandpass interval of the frequency spectrum with bandwidth B centered on ω . As the interval is single sided, we must use complex valued quantities to represent it.

We wish to simulate a bandpass AWGN channel at baseband ($\omega = 0$). This implies a frequency shift of the complex valued signal, but the signal remains complex valued and it's power is unchanged. The negative frequency component on the LHS of Figure 1 is redundant and after frequency shifting can be removed by filtering.

Note that even at baseband we must use complex valued quantities for the signal and noise to represent a bandpass signal of bandwidth B . For example, given a fixed sample rate B and noise power N , a real valued noise sequence can only represent a bandwidth of $B/2$ which results in doubling the noise density $N_0 = N/(B/2) = 2N_0$ compared to a complex valued noise sequence with the same power.

The energy of each BPSK symbol E_b is the signal power S divided by the symbol rate $R_b = 1/T_b$. The noise per unit bandwidth is the total noise power N divided by the bandwidth B of the system. If we are simulating at one sample per symbol, $B = R_b$:

$$\begin{aligned}\frac{E_b}{N_0} &= \frac{S/R_b}{N/R_b} \\ &= \frac{S}{N} \\ &= \frac{A^2}{\sigma^2}\end{aligned}\tag{3}$$

where A is the amplitude of each BPSK symbol and $\sigma^2 = N$ is the variance of the complex valued noise (mean noise energy per sample). Given a set point E_b/N_0 :

$$\sigma = \frac{A}{\sqrt{E_b/N_0}}\tag{4}$$

The complex noise sample r_i can be generated as:

$$r_i = \frac{\sigma}{\sqrt{2}}(\mathcal{N}_{2i}(0, 1) + j\mathcal{N}_{2i+1}(0, 1))\tag{5}$$

where $\mathcal{N}_i(0, 1)$ is the i -th sample of a unit variance, zero mean, real Gaussian noise source. Note the noise power is split evenly between the real and imaginary arms. Our symbols passing through an AWGN channel can be simulated at complex baseband as:

$$\begin{aligned}\hat{z}_i &= z_i + r_i \\ \hat{q}_i &= q_i + r_i\end{aligned}\tag{6}$$

If the noise is zero mean, we can estimate σ^2 over K noise samples r_i as:

$$\sigma^2 = E[|r_i|^2] = \frac{1}{K} \sum_{i=0}^{K-1} |r_i|^2\tag{7}$$

1.1 SNR Measurement

In order to compare with other methods of speech communication that have varying bandwidths B , it is useful to formulate expressions for estimating SNR from the BPSK and QPSK symbols. The Signal to Noise ratio (SNR) is given by:

$$\begin{aligned}\frac{S}{N} &= \frac{E_b R_b}{N_0 B} \\ &= \frac{E_q R_q}{N_0 B}\end{aligned}\tag{8}$$

A noise bandwidth B needs to be selected; common choices are $B = R_b$, in which case $S/N = E_b/N_0$; for HF radio $B = 3000$ Hz to compare with existing analog and digital voice waveforms; or $B = 1$ to obtain a normalised C/N_0 carrier power to noise density ratio - useful for comparing waveforms with different bandwidths.

At one sample per symbol, the power, the mean energy of each QPSK symbol over a window of K samples is given by:

$$E_q = E[|q_i|^2] = \frac{1}{K} \sum_{i=0}^{K-1} |q_i|^2 \quad (9)$$

Note the variance function should not be used to calculate E_q , as we cannot guarantee q_i is zero mean. As each QPSK symbol contains 2 BPSK symbols, the energy is split evenly:

$$E_b = E_q/2 \quad (10)$$

For example if the symbol amplitude is $A = 1$, $E_b = A^2 = 1$, then $E_q = 1+1 = 2$.

To model transmission over multipath channels using OFDM we arrange the QPSK symbols as N_c parallel carriers, each running at a symbol rate of $R_s = R_q/N_c$ symbols/s, where R_s is chosen based on delay spread considerations. Typical values for HF modems are $N_c = 20$ and $R_s = 50$ Hz. However the OFDM carriers are arranged such that the total symbol rate over the channel remains constant. So for a given signal power E_q and E_b remain constant (Table 1).

Waveform	N_c	R_s	R_q	R_b	E_q	E_b
Single Carrier BPSK	1	-	-	2000	-	$S/2000$
Single Carrier QPSK	1	-	1000	2000	$S/1000$	$S/2000$
OFDM QPSK	20	50	1000	2000	$S/1000$	$S/2000$

Table 1: E_b and E_q examples for single and multi-carrier OFDM waveforms for constant carrier power S

1.2 Calibration and Testing

In order to evaluate the ML system early in the development process it is important to ensure the noise is correctly calibrated. The expressions above can be used to check the noise injection process:

1. Set a target E_b/N_0 for the simulation run, and calculate σ using (4).
2. Establish the equivalent target SNR from (8) evaluated using the target E_b/N_0 .
3. After the simulation run measure $E_q = E[|q_i|^2]$ over a sample of transmitted symbols. Note that in general $E_q \neq 2$ as the encoder outputs continuous values.

4. Calculate measured SNR using (8) and compare.

The calibration of the noise injection can be checked by replacing the encoder output z_i with discrete PSK symbols to create a digital modem, then measuring the BER at E_b/N_0 points. The theoretical BER over an AWGN channel is:

$$BER = 0.5 \operatorname{erfc}(\sqrt{E_b/N_0}) \quad (11)$$

For a multipath channel:

$$BER = 0.5 \left(1 - \sqrt{\frac{E_b/N_0}{E_b/N_0 + 1}} \right) \quad (12)$$

2 Over the Cable and Over the Air Tests

Impressive results have been obtained from the symbol rate simulations of an OFDM modem. These assumed ideal synchronisation. We would like to verify these results using real radio signals in Over The Cable (OTC) and Over the Air (OTA) tests. This requires building up a rate Fs_s system, and synchronisation subsystems. For a first pass, the choice was made to use classical DSP pilot symbol based synchronisation, although we acknowledge potential for ML based synchronisation in future iterations.

The goal is to compare speech quality to SSB at $E_b/N_0 = 0dB$ (approx -3dB SNR in a 3000Hz BW), and work through any issues that prevent the system working over real radio channels. PAPR will be ignore for the first pass tests, as we are mainly concerned with verifying the low E_b/N_0 results suggested by the symbol rate simulations.

Pilot symbols have been inserted into each OFDM carrier at a rate of one pilot every 4 data symbols. From [1], the SNR loss from injecting the pilot symbols is given by:

$$L_p = 10 \log_{10} \frac{N_s}{N_s - 1} \quad (13)$$

For $N_s = 5$, the loss is 0.96dB. To maintain the same payload symbol rate over the channel, the bandwidth increases:

$$R'_b = R_b \frac{N_s}{N_s - 1} \quad (14)$$

For $N_s = 5$, $R'_b = 2500$ symbols/s, or a OFDM QPSK bandwidth of around 1250 Hz plus some guard bandwidth.

A pilot based sync system was built in PyTorch, and is used for coarse and fine timing, phase and amplitude equalisation. Unlike regular PSK, the ML network is likely to be sensitive to amplitude variations. Phase equalisation also allows small frequency offsets (± 2 Hz) to be tracked.

Several phase estimators were prototyped, and tested using BER measurements. Maintaining low loss synchronisation at low E_b/N_0 is challenging. As

further work a lower latent dimension d and higher E_b/N_0 , would allocate more power to pilots, and result in less carriers. Using per-carrier phase estimation makes the system less dependant on fine timing accuracy and gives us the ability to handle multipath, but has higher loss than algorithms that consider all carriers at the same time.

Figure 2: OFDM pilot based synchronisation algorithm performance, tested with digital PSK symbols on an AWGN channel. With ideal sync, intelligible speech is produced at $E_b/N_0 = -6$ dB or BER=0.24.

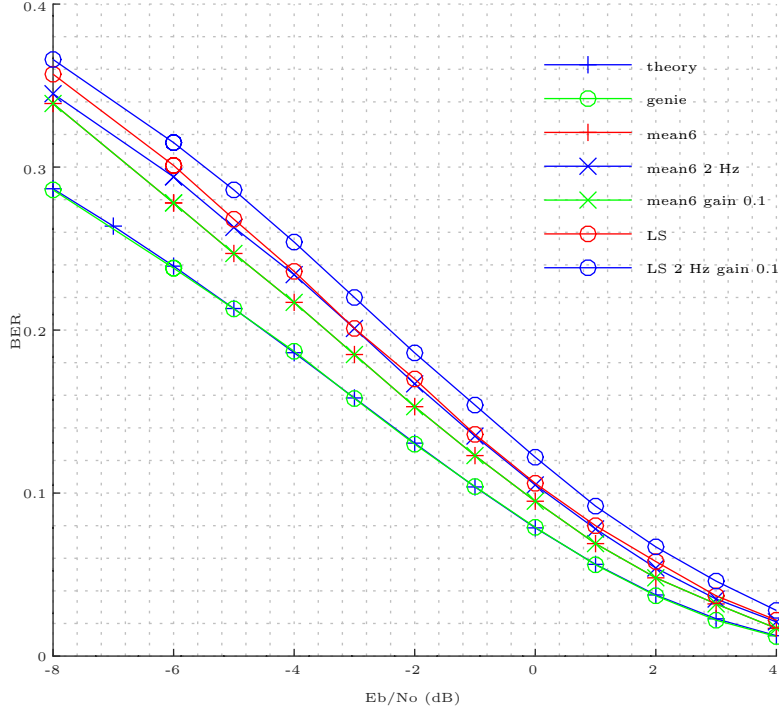


Figure 2 plots the performance of the OFDM pilot based synchronisation system used for the OTC/OTA tests on an AWGN channel. The unusually low E_b/N_0 range we are considering is challenging. The *genie* curve is the baseline rate F_s OFDM system with ideal sync, and matches the theoretical results. Using this system, we can obtain intelligible speech at $E_b/N_0 = -6$, or BER=0.24 in a digital system. We can use the BER=0.25 line to estimate the loss of the synchronisation based system at this operating point, which for the *mean6* and *LS* algorithms under realistic conditions is around 2 to 2.4 dB. The

LS works better on fast fading multipath channels.

Combined with L_p , we estimate a total sync loss of 3dB for this first pass of the ML system combined with classical pilot based synchronisation. However we note that no cyclic prefix has been added at this time.

TODO Figure of OFDM frame. TODO Block diagram of OTC tests
Further work:

1. Try a low dimesnions latent vector, e.g. $d = 40$, and see if similar speech quality can be obtained at 3dB high E_b/N_0 . This would result in lower sync losses, as the E_b/N_0 of the pilots would be increased. Does the encoder output still resemble BPSK, or is it training to a higher order constellation?
2. Attempt to use the ML network to perform frequency, phase and amplitude equalisation, wither with or without passing the pilots to the decoder. Some initial results without pilots resultyng in some performance degradation, however this may be acceptable if it is in the same order as the pilot based sync losses. Some pilot or unique word injection may still be required to perform coarse and fine timing estimation using classical DSP running at the sample rate.
3. Work to improve the current classical DSP sync, e.g. a feedback loop to track out frequency offsets is worth 1 dB.
4. Include PAPR optimisation and rate F_s multipath channels in the training.

3 Comparison with Other Speech Waveforms

We wish to compare our radio autoencoder with existing waveforms used for speech transmission over radio channels. We start with the assumption that we have a transmitter of C watts, and an AWGN channel with a spectral noise density of N_0 watts/Hz. As the speech waveforms being considered vary in bandwidth we will choose C/N_0 as the SNR metric.

The C/N_0 (in dBHz) at the demodulator input of a terrestrial radio receiver is given by:

$$\frac{C}{N_0} = P - PAPR - L_{path} - NF + 174 \quad (15)$$

where P is the maximum output power of the transmitter power amplifier, $PAPR$ is the Peak to Average Power Ratio of the waveform, L_{path} is the path loss, NF is the noise figure of the receiver. For example consider a 400 MHz FM hand held radio over a 1km urban (non line of site) path. The radio has a 1W (30 dBm) power output, $L_{path} = 120$ dB, with noise dominated by ambient EMI such that $NF = 10$ dB. $C/N_0 = 30 - 0 - 120 - 10 + 174 = 74$ dBHz, sufficient for good quality speech (Table 5).

Note that C/N_0 at the demodulator is a function of PAPR. A high PAPR reduces the C/N_0 at the receiver. We effectively “back off” the transmitter

power from the maximum P by the PAPR. We assume the PA is capable of sustaining P watts indefinitely. As PAPR varies by waveform, it should be included in any metric for comparison of waveforms. We define P/N_0 as:

$$P/N_0 = C/N_0 + PAPR \quad (16)$$

A waveform that delivers intelligible speech at a low P/N_0 is the target. A low PAPR waveform has other desirable properties, such as greater PA efficiency, longer battery life, and low cost semiconductors.

Waveform	Threshold
Single Sideband	0dB SNR in 3000Hz noise BW, 2400Hz audio bandwidth, Tx speech compressor with 6dB PAPR
Frequency Modulation	-120 dBm quoted for many NBFM radios, 54dB above -174dBm/Hz noise floor
FreeDV 700D	10% PER threshold at -2dB SNR in 3000Hz noise BW
Radio Autoencoder	Intelligible speech at $E_b/N_0 = -6$ dB, $R_b = 2000$ symbols/s, 3dB sync overhead

Table 2: Thresholds for speech link closure for each waveform. The link is considered closed when the speech is barely intelligible to a trained listener.

Waveform	Threshold C/N_0 calculations (dBHz)
Single Sideband	$0 + 10\log_{10}(3000) = 35$
Frequency Modulation	$-120 + 174 = 54$
FreeDV 700D	$-2 + 10\log_{10}(3000) = 33$
Radio Autoencoder	$-6 + 10\log_{10}(2000) + 3 = 30$

Table 3: Threshold C/N_0 calculations.

Waveform	Abbr	RF BW	PAPR	C/N_0	P/N_0	Δ
Single Sideband	SSB	2400	6	35	41	-10
Frequency Modulation	NBFM	16000	0	54	54	-23
FreeDV 700D	700D	1100	4	33	37	-6
Radio Autoencoder	radAE	1400	1	30	31	0

Table 4: Comparison of link closure by waveform over AWGN channels.

Waveform	Audio BW	C/N_0	P/N_0	Δ
Radio Autoencoder	8000	36	37	0
Frequency Modulation	3000	64	64	-27
Single Sideband	2000	55	61	-24

Table 5: Comparison of good quality “arm chair copy” by speech waveform over AWGN channels. They are ranked in terms of maximum achievable speech quality. FreeDV 700D has been omitted because of its low speech quality even in ideal channels. The radio autoencoder delivers wideband (8000 Hz) audio.

4 Glossary

Symbol	Explanation	Units
B	noise or signal bandwidth	Hz
C	Carrier (transmitter) power $C = S$ for this study	
C/N_0	Carrier power/spectral noise density	
d	dimension of latent vector \mathbf{z}	
E_b/N_0	energy per BPSK symbol on spectral noise density	
E_q/N_0	energy per QPSK symbol on spectral noise density	
N	total noise power	Watts
N_c	Number of carriers	
N_0	Noise power in 1 Hz of bandwidth	
P/N_0	Peak trasnmmitter power/spectral noise density	
\mathbf{q}	vector of QPSK symbols	
q_i	single QPSK symbol, element of \mathbf{q}	
R_b	BPSK symbol rate	symbols/second
R_q	QPSK symbol rate	symbols/second
R_s	OFDM per carrier QPSK symbol rate	symbols/second
R_z	latent vector update rate	Hz
SNR	signal to noise Ratio	
S	total signal (carrier) power	Watts
T_b	BPSK symbol period	seconds
T_q	QPSK symbol period	seconds
T_s	OFDM per carrier QPSK symbol period	seconds
T_z	time between latent vector updates	seconds
r_i	noise sample	
\mathbf{z}	Autoencoder output latent vector	
z_i	single latent vector element of \mathbf{z} , a BPSK symbol	

Table 6: Glossary of Symbols

5 References

- [1] Low SNR FreeDV Modes. <https://github.com/drowe67/misc/blob/>

master/freedv_low/freedv_low.pdf.