

EE 102 Week 11, Lecture 1 (Fall 2025)

Note: The last two sections of this document will be covered in lecture 2.

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1 Announcements

- HW #10 is due on Mon Nov 17.
- HW #11 will be released Tue Nov 18 and due on Mon Nov 24.

2 Goals

By the end of this lecture, you should be able to understand the process of sampling a continuous-time signal and how the original signal can be reconstructed from the discrete samples. You will learn to distinguish between the sampling rate, the frequency of the original signal, and the frequencies in the sampled signal. Finally, you will be able to understand that if you keep on increasing the number of samples for a signal, your reconstructed signal will get closer and closer to the original signal. The lower number of samples you take, the more distorted your reconstructed signal will be. But there is a minimum number of samples you must take in order to capture all frequency information of the original signal without distortion. This minimum sampling rate is called the Nyquist rate.

3 Introduction to Sampling: A Cosine Example

In this section we connect what you saw in the in-class activity (sampling different signals at different rates) to the frequency-domain view of sampling and the Nyquist rate. We will use a single cosine as our starting point:

$$x(t) = \cos(\omega_0 t),$$

where ω_0 is the angular frequency in rad/s.

The process that we will follow will start by writing the sampled signal in time-domain using impulses. Then, to meet our learning goal of understanding the frequency-domain view of sampling — that is, we want to find out the minimum number of samples needed to capture all frequency information of the original signal without distortion — we will derive the Fourier transform of the sampled signal. Using the frequency domain representation of the sampled signal, we will be able to comment on the minimum sampling rate needed and any other extra steps needed to ensure that we can reconstruct the original signal's frequencies without distortion.

3.1 Sampling in time using an impulse train

A continuous-time signal $x(t)$ is sampled every T_s seconds. The sampling instants are

$$t_n = nT_s, \quad n = 0, \pm 1, \pm 2, \dots$$

The sampled signal can be written in continuous time as a train of weighted impulses:

$$x_s(t) = \sum_{n=-\infty}^{\infty} x(nT_s) \delta(t - nT_s). \quad (1)$$

This expression comes directly from the **sifting property** of the impulse that we have discussed before:

$$\int_{-\infty}^{\infty} x(t) \delta(t - t_0) dt = x(t_0).$$

Each term $x(nT_s) \delta(t - nT_s)$ is zero everywhere except at $t = nT_s$, and if we integrate $x_s(t)$, only those points contribute. So, the summation above holds.

Pop Quiz 3.1: Check your understanding!

Define the sampling period T_s , the seconds between samples, on a graph. Find out the sampling frequency F_s (in Hz) and the sampling angular frequency ω_s (in rad/s) using T_s .

Solution on page 8

Our goal is to reconstruct the original frequency content of $x(t)$, in this case, the cosine frequency ω_0 , from the sampled signal $x_s(t)$. To do this, we will analyze the frequency-domain representation of the sampled signal $x_s(t)$ next.

Fourier transform of the sampled signal

The signal that we are interested in finding the frequency domain representation of is the sampled signal: $x_s(t)$. Specifically, we want to see whether the frequency domain representation of the sampled signal $X_s(\omega)$ contains the original frequency ω_0 of the cosine signal $x(t) = \cos(\omega_0 t)$, and if so, under what conditions (how many samples do we need to ensure that we get the original frequency ω_0 in $X_s(\omega)$ without any distortion). We will do this in several steps.

3.1.1 Fourier transform of the original cosine

First, we look at the Fourier transform of the original cosine signal $x(t) = \cos(\omega_0 t)$. Using Euler's relation we can write the cosine as a sum of complex exponentials:

$$\cos(\omega_0 t) = \frac{1}{2} (e^{j\omega_0 t} + e^{-j\omega_0 t}).$$

Now, using the CTFT definition

$$X(\omega) = \int_{-\infty}^{\infty} x(t) e^{-j\omega t} dt,$$

we know the transform of complex exponentials:

$$\mathcal{F}\{e^{j\omega_0 t}\} = 2\pi \delta(\omega - \omega_0), \quad \mathcal{F}\{e^{-j\omega_0 t}\} = 2\pi \delta(\omega + \omega_0).$$

Therefore, for $x(t) = \cos(\omega_0 t)$,

$$X(\omega) = \frac{1}{2} [2\pi \delta(\omega - \omega_0) + 2\pi \delta(\omega + \omega_0)] = \pi [\delta(\omega - \omega_0) + \delta(\omega + \omega_0)].$$

So the spectrum of a cosine consists of two impulses, one at $+\omega_0$ and one at $-\omega_0$.

3.1.2 Fourier transform of a train of impulses

Now we need the Fourier transform of a periodic impulse train, which we use to model the sampling process. Note that we have the train of impulse signal

$$p(t) = \sum_{n=-\infty}^{\infty} \delta(t - nT_s)$$

multiplied with the original signal $x(t)$ to get the sampled signal $x_s(t)$ (see equation (1)). This is a train of impulses spaced T_s seconds apart. We observe that $p(t)$ is periodic in time with period T_s since

$$p(t + T_s) = p(t) \quad \text{for all } t.$$

Pop Quiz 3.2: Check your understanding!

Plot the train of impulse signal $p(t)$. Visually and mathematically verify that $p(t)$ is periodic with period T_s .

Solution on page 8

Because $p(t)$ is periodic, we can represent it as a sum of complex exponentials using its Fourier series. This will help us compute its Fourier transform more easily. We have

$$p(t) = \sum_{k=-\infty}^{\infty} c_k e^{jk\omega_s t}, \quad \text{with} \quad \omega_s = \frac{2\pi}{T_s},$$

and the Fourier series coefficients are

$$c_k = \frac{1}{T_s} \int_0^{T_s} p(t) e^{-jk\omega_s t} dt,$$

Recall from [Homework #6 Problem 1](#) that the Fourier series coefficients for a periodic impulse train is

$$c_k = \frac{1}{T_s} \quad \text{for all } k, \quad \text{so} \quad p(t) = \frac{1}{T_s} \sum_{k=-\infty}^{\infty} e^{jk\omega_s t}.$$

Now we take the Fourier transform of $p(t)$. Using linearity:

$$P(\omega) = \mathcal{F}\{p(t)\} = \frac{1}{T_s} \sum_{k=-\infty}^{\infty} \mathcal{F}\{e^{jk\omega_s t}\}.$$

From [Pop quiz 3.1 in week 11 lecture 1](#), we know that the Fourier transform of a complex exponential is

$$\mathcal{F}\{e^{j\omega_0 t}\} = 2\pi \delta(\omega - \omega_0).$$

Here, $\omega_0 = k\omega_s$, so

$$\mathcal{F}\{e^{jk\omega_s t}\} = 2\pi \delta(\omega - k\omega_s).$$

Therefore

$$P(\omega) = \frac{2\pi}{T_s} \sum_{k=-\infty}^{\infty} \delta(\omega - k\omega_s).$$

So, finally, we can write that the Fourier transform of a periodic impulse train with period T_s is a train of impulses in the frequency domain (how convenient!)! The impulses in the frequency domain are spaced by $\omega_s = \frac{2\pi}{T_s}$ — the sampling frequency. So, we have the pair:

$$p(t) = \sum_{n=-\infty}^{\infty} \delta(t - nT_s) \quad \Longleftrightarrow \quad P(\omega) = \frac{2\pi}{T_s} \sum_{k=-\infty}^{\infty} \delta(\omega - k\omega_s).$$

Now are ready to compute the Fourier transform of the sampled signal $x_s(t)$.

Fourier transform of the sampled signal: multiplication of $p(t)$ and $x(t)$

Sampling a signal $x(t)$, as in equation (1), can be viewed as multiplying the original signal $x(t)$ by the impulse train $p(t)$. How? See below:

$$x_s(t) = x(t) p(t) = x(t) \sum_{n=-\infty}^{\infty} \delta(t - nT_s) = \sum_{n=-\infty}^{\infty} x(t) \delta(t - nT_s).$$

Using the sifting property inside the sum:

$$x_s(t) = \sum_{n=-\infty}^{\infty} x(nT_s) \delta(t - nT_s),$$

which matches our original expression in equation (1). Now, our goal is to compute the frequency domain representation of the sampled signal $x_s(t)$ by computing its Fourier transform.

In the frequency domain, multiplication in time corresponds to *convolution* in frequency. We have not seen this explicitly but you may get the intuition for why this holds true from the duality between time and frequency domains. Specifically, recall that when we convolve two signals in time domain, that is, if we have $y(t) = x(t) * h(t)$, then in the frequency domain, we have $Y(\omega) = X(\omega)H(\omega)$ — multiplication in frequency! So, by duality, it holds true that multiplication in time corresponds to convolution in frequency. You may find a proof of this property in Chapter 4 of Oppenheim and Willsky's Signals and Systems textbook (2nd Edition). We use this property here to compute the Fourier transform of the sampled signal $x_s(t)$. We have

$$X_s(\omega) = \frac{1}{2\pi} [X(\omega) * P(\omega)],$$

where $X(\omega)$ and $P(\omega)$ are the Fourier transforms of $x(t)$ and $p(t)$ respectively (the $1/2\pi$ factor comes from the multiplication property of the Fourier transform) Now, substituting $P(\omega)$, we have

$$X_s(\omega) = \frac{1}{2\pi} X(\omega) * \left(\frac{2\pi}{T_s} \sum_{k=-\infty}^{\infty} \delta(\omega - k\omega_s) \right) = \frac{1}{T_s} \left[X(\omega) * \sum_{k=-\infty}^{\infty} \delta(\omega - k\omega_s) \right].$$

Again, recall a property of Fourier transforms that the convolution with a shifted delta shifts the function. So,

$$X(\omega) * \delta(\omega - a) = X(\omega - a).$$

$$X_s(\omega) = \frac{1}{T_s} \sum_{k=-\infty}^{\infty} X(\omega - k\omega_s).$$

Therefore, we get that the frequency domain representation of the sampled signal $X_s(\omega)$ is a scaled sum of shifted copies of the original spectrum $X(\omega)$ (not ideal!), shifted by multiples of ω_s .

For our cosine example, we have already computed $X(\omega)$:

$$X(\omega) = \pi[\delta(\omega - \omega_0) + \delta(\omega + \omega_0)]$$

which gives us

$$X_s(\omega) = \frac{1}{T_s} \sum_{k=-\infty}^{\infty} X(\omega - k\omega_s) = \frac{1}{T_s} \sum_{k=-\infty}^{\infty} \pi[\delta(\omega - k\omega_s - \omega_0) + \delta(\omega - k\omega_s + \omega_0)].$$

So $X_s(\omega)$ has impulses at

$$\omega = \pm\omega_0 + k\omega_s, \quad k \in \mathbb{Z}.$$

The original two impulses at $\pm\omega_0$ are now repeated (copied) at integer multiples of the sampling frequency ω_s !!! This is not great, because now the sampled signal contains many more frequency components than the original signal (these are the distortions that you hear when you don't sample correctly!). How can we remove these additional impulses and recover the original cosine frequency ω_0 ? Low pass filtering! We will discuss this in more detail next time.

Next class: Filtering to remove distortions

The original continuous-time cosine only had two impulses at $\omega = \pm\omega_0$. After sampling, $X_s(\omega)$ contains infinitely many impulses, at

$$\omega = \pm\omega_0, \quad \pm\omega_0 \pm \omega_s, \quad \pm\omega_0 \pm 2\omega_s, \quad \dots$$

If ω_s is large enough, these copies are separated in frequency and do not overlap. But if ω_s is too small, the shifted impulses can collide or cross into each other. In other words, impulses from different “copies” of $X(\omega)$ may end up in the same frequency location. This leads to distortion in the reconstructed signal called aliasing.

What is aliasing? When the sampling frequency is too low, different frequency components in the original signal produce overlapping or indistinguishable contributions in the sampled spectrum. In the reconstructed signal, these contributions appear as *fake* or *misplaced* frequencies. This phenomenon is called **aliasing**: different original frequencies become indistinguishable after sampling.

For a single cosine, aliasing means that a high-frequency cosine can “look like” a lower-frequency cosine once sampled, because their impulses line up after shifts by ω_s .

As we said above, to reconstruct the original continuous-time signal $x(t)$ from its samples, we may design a low-pass filter to remove the extra copies in $X_s(\omega)$. This will work only if the copies do not overlap with the original spectrum. An ideal low-pass filter has a cutoff frequency ω_c that passes only the frequency band containing the original $X(\omega)$ (from $-\omega_c$ to $+\omega_c$) and removes all higher frequencies will work well.

For a single cosine at ω_0 , we can choose the cutoff frequency ω_c such that

$$\omega_0 < \omega_c < \omega_s - \omega_0.$$

This is possible *only if* the original impulse at $+\omega_0$ is strictly separated from the nearest shifted impulse at $\omega_s - \omega_0$. That gives the inequality

$$\omega_0 < \omega_s - \omega_0 \iff \omega_s > 2\omega_0.$$

Under this condition, an ideal low-pass filter with passband $|\omega| < \omega_c$ will keep the original impulses at $\pm\omega_0$ and completely remove all impulses from the shifted copies. In the time domain, this low-pass filter reconstructs the original continuous-time cosine $x(t) = \cos(\omega_0 t)$ from the samples (our overall goal!). The condition that we just obtained is called the **Nyquist sampling condition**.

We have shown that to avoid overlap between the original impulses at $\pm\omega_0$ and the nearest replicated impulses (at $\pm\omega_0 \pm \omega_s$), we must have

$$\omega_s > 2\omega_0.$$

We can obtain an equivalent relation in Hz. Recall $\omega_s = \frac{2\pi}{T_s}$ and $\omega_0 = 2\pi f_0$ where f_0 is the ordinary frequency in Hz. In terms of the sampling frequency $F_s = 1/T_s$:

$$\omega_s > 2\omega_0 \iff 2\pi F_s > 2(2\pi f_0) \iff F_s > 2f_0.$$

So, the Nyquist rate for a single cosine:

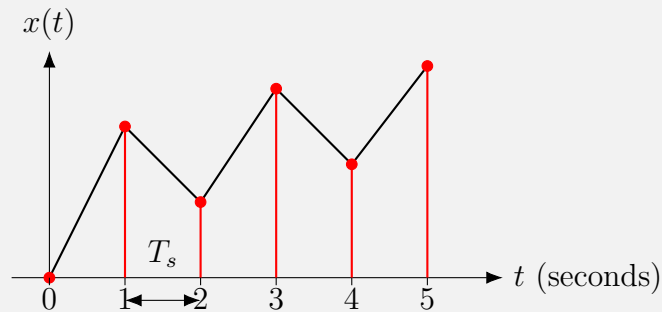
$$F_s > 2f_0, \quad f_0 = \frac{\omega_0}{2\pi}.$$

If we sample *above* this Nyquist rate, we can in principle use an ideal low-pass filter to remove the extra copies in $X_s(\omega)$ and reconstruct the original cosine exactly from its samples. This is the key result of this week’s theoretical topics.

Pop Quiz Solutions

Pop Quiz 3.1: Solution(s)

The sampling period T_s is the time interval between two consecutive samples. See the graph below for reference:



The sampling frequency F_s is the number of samples taken per second, which is the reciprocal of the sampling period:

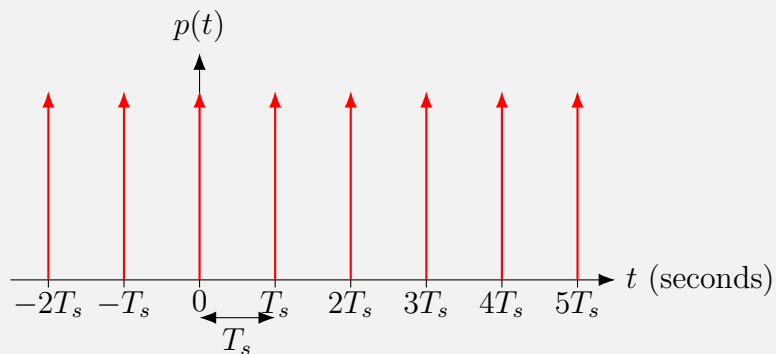
$$F_s = \frac{1}{T_s} \quad [\text{samples/second}].$$

The sampling angular frequency is

$$\omega_s = 2\pi F_s = \frac{2\pi}{T_s}.$$

Pop Quiz 3.2: Solution(s)

The plot of the train of impulse signal $p(t)$ is shown below:



To verify that $p(t)$ is periodic with period T_s , we check that $p(t + T_s) = p(t)$ for all t :

$$p(t + T_s) = \sum_{n=-\infty}^{\infty} \delta(t + T_s - nT_s) = \sum_{n=-\infty}^{\infty} \delta(t - (n - 1)T_s).$$

By changing the index of summation from n to $m = n - 1$, we have

$$p(t + T_s) = \sum_{m=-\infty}^{\infty} \delta(t - mT_s) = p(t).$$