

VLSI Implementation of a Pipelined 128 points 4-Parallel radix-2³ FFT Architecture via Folding Transformation

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Digital Signal Processing in Very Large Scale Integration Systems

Autumn 2019

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Abstract— In this work we present a develop and VLSI implementation of a 4-parallel pipelined architecture for the complex fast Fourier transform (CFFT) based on the radix-2³ algorithm with 128 points using folding transformation and register minimization techniques. In addition, we are going to generate different synthesis levels from the hardware language description (HDL) with the purpose of obtaining a suitable performance on speed and area using standard cells at 45nm.

I. INTRODUCTION

The Fast Fourier Transform (FFT) is widely used in different applications fields, particularly, it is used in algorithms that involves apply digital signal processing, e.g., calculate the Discrete Fourier Transform (DFT) efficiently, that is useful because in some applications is most convenient to work in frequency domain than time domain. Nowadays is common utilize the algorithm of FFT for real time applications and parallel-pipelined hardware architecture give us the opportunity to work at high throughput rates.

There are two main types of pipelined FFT architectures [1]. On the one hand, feedback architectures (FB) which can be divided into Single-path Delay Feedback (SDF) and Multi-path Delay Feedback (MDF), these methods take out samples from each butterflies stages and feed back to the registers or memories at the same stage. On the other hand, feedforward architectures such as Multi-Path Delay Commutator (MDC) where the main difference with the feedback architectures is that SDF transfer data samples from one stage to other stage serially, instead of that the MDC architecture transfer more than one sample per clock cycle and do not have feedback loops.

This work focuses on the design of 4-parallel pipelined architecture radix-2³ 128-points for Complex FFT-DIF (Decimation in frequency). First, we will obtain the equations that correspond to Butterfly structure of radix-2³ FFT-DIF for 8 points. After that, we apply these idea to design a 2-parallel pipelined architecture radix-2³ 16-points FFT via folding transformation and find the appropriate (*twiddle factors*) for each stage and clock cycle over the chain of butterflies on a feedforward architecture MDC. Finally we traslate this to a 128-points model.

Later we elaborate a float-point simulator in *Matlab* of the 128-points model which will process a summation of two cosine signals with different frequencies. After that, for the input and output of each stage of DFT, we quantized all operations such as adders and multipliers to get a fixed-point model. In this way, we can compare both models verifying the Signal to quantization noise ratio (SQNR) between fixed and float models.

Furthermore, we take the fixed-point model to elaborate a Synthesizable Verilog code HDL and verify the DFT functionality in each stage of the architecture. In addition to this, we generates power-area-timing report with different optimizations such as varying pipelining levels and canonical signed digit (CSD) to get a clock frequency of 500Mhz.

II. THE RADIX-2³ FFT ALGORITHM

The N -point DFT of an input sequence $x[n]$ is defined as:

$$X[k] = \sum_{n=0}^{N-1} x[n] \dot{W}_N^{nk}, \quad k = 0, 1, \dots, N-1 \quad (1)$$

where $\dot{W}_N^{nk} = e^{-j\frac{2\pi}{N}nk}$.

The FFT based on Cooley-Tukey algorithm is most commonly used in order to compute the DFT efficiently, this allows us reduce the number of operations from $O(N^2)$ for the DFT to $O(N \log_2 N)$ for the FFT. Direct computation of the DFT is basically inefficient primarily because it does not exploit the symmetry and periodicity properties of the phase factor W_N , these two properties are:

$$\text{Symmetry property: } W_N^{k+N/2} = -W_N^k \quad (2)$$

$$\text{Periodicity property: } W_N^{k+N} = W_N^k \quad (3)$$

The development of computationally efficient algorithms for DFT is possible if we adopt a *Divide and Conquer* approach. This approach is based on the decomposition of an N point DFT into successively smaller DFTs. In accordance with this, the DFT is calculated in series of $s = \log_\rho N$ stages, where ρ is the base of the *radix*. In our work this factor is two because we need to design a radix-2³ FFT and this kind of radix is built using as principal base *radix*-2.

There are two methods to design FFT algorithms [2], [3]:

First, applying decimation in time (DIT), this results in a split of the N -point data sequence $x[n]$ into two $N/2$ -point data sequences. Thus, we can obtain two different functions by decimating $x[n]$ by a factor of 2. The decimation of the data sequence can be repeated again and again until the resulting sequences are reduced to one-point sequence. In each decomposition, the basic computing unit that processes the samples is called *butterfly*.

Second, the decimation in frequency algorithm, is obtained by using the divide-and-conquer approach. To derive the algorithm we begin by splitting the DFT formula into two summations, one of which involves the sum over the first $N/2$ data points and the second sum involves the last $N/2$ data points

In general, each butterfly involves one complex multiplication and two complex additions. The main difference that we can see in Fig.1 between DIT and DIF is the instant in which the multiplication by W_N^ϕ is accomplished, it means, the input samples can be multiplied before or after of split and add internally the samples inside the butterfly structure.

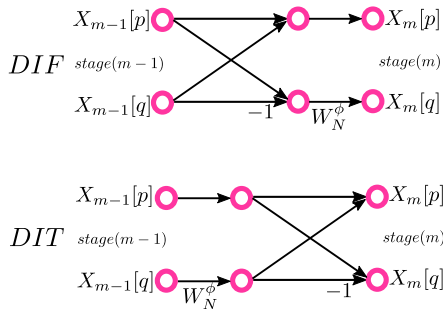


Figure 1: Basic butterflies computation in the decimation in time and frequency.

In addition, the input samples in FFT algorithms DIF are organized in natural order but its output has not in order, in this case is necessary a circuit for reordering the output data. On the other hand, FFT algorithms DIT is all the opposite, It has not its input in order and its output has a natural order.

Following the methodology presented in [2], we can understand and apply the mathematical expressions of *radix*-2³ DIF explained in [4].

These fundamental equations are:

$$\begin{aligned} C_{8k+0} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n + x_{n+\frac{N}{2}}) + (x_{n+\frac{N}{4}} + x_{n+\frac{3N}{4}})] + \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} + x_{n+\frac{5N}{8}}) + (x_{n+\frac{3N}{8}} + x_{n+\frac{7N}{8}})] \right\} W_N^{0n} W_N^{nk} \quad (4) \\ C_{8k+4} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n + x_{n+\frac{N}{2}}) + (x_{n+\frac{N}{4}} + x_{n+\frac{3N}{4}})] - \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} + x_{n+\frac{5N}{8}}) + (x_{n+\frac{3N}{8}} + x_{n+\frac{7N}{8}})] \right\} W_N^{4n} W_N^{nk} \\ C_{8k+2} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n + x_{n+\frac{N}{2}}) - (x_{n+\frac{N}{4}} + x_{n+\frac{3N}{4}})] - j \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} + x_{n+\frac{5N}{8}}) - (x_{n+\frac{3N}{8}} + x_{n+\frac{7N}{8}})] \right\} W_N^{2n} W_N^{nk} \\ C_{8k+6} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n + x_{n+\frac{N}{2}}) - (x_{n+\frac{N}{4}} + x_{n+\frac{3N}{4}})] + j \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} + x_{n+\frac{5N}{8}}) - (x_{n+\frac{3N}{8}} + x_{n+\frac{7N}{8}})] \right\} W_N^{6n} W_N^{nk} \\ C_{8k+1} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n - x_{n+\frac{N}{2}}) - j(x_{n+\frac{N}{4}} - x_{n+\frac{3N}{4}})] + W_N^{N/8} \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} - x_{n+\frac{5N}{8}}) - j(x_{n+\frac{3N}{8}} - x_{n+\frac{7N}{8}})] \right\} W_N^n W_N^{nk} \\ C_{8k+5} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n - x_{n+\frac{N}{2}}) - j(x_{n+\frac{N}{4}} - x_{n+\frac{3N}{4}})] - W_N^{N/8} \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} - x_{n+\frac{5N}{8}}) - j(x_{n+\frac{3N}{8}} - x_{n+\frac{7N}{8}})] \right\} W_N^{5n} W_N^{nk} \\ C_{8k+3} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n - x_{n+\frac{N}{2}}) + j(x_{n+\frac{N}{4}} - x_{n+\frac{3N}{4}})] + W_N^{3N/8} \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} - x_{n+\frac{5N}{8}}) + j(x_{n+\frac{3N}{8}} - x_{n+\frac{7N}{8}})] \right\} W_N^{3n} W_N^{nk} \\ C_{8k+7} &= \sum_{n=0}^{N/8-1} \left\{ [(x_n - x_{n+\frac{N}{2}}) + j(x_{n+\frac{N}{4}} - x_{n+\frac{3N}{4}})] - W_N^{3N/8} \right. \\ &\quad \left. [(x_{n+\frac{N}{8}} - x_{n+\frac{5N}{8}}) + j(x_{n+\frac{3N}{8}} - x_{n+\frac{7N}{8}})] \right\} W_N^{7n} W_N^{nk} \end{aligned}$$

In Fig. 2 and Fig. 3 we represent the equivalent diagram of interconnections and data flows from the equations presented in (4).

The use of higher value radices lead to different amount of rotators. If we compare the quantity of rotators of an architecture *radix*-2 FFT with an architecture *radix*-2^k FFT, this last has less number of phase factors than use a *radix*-2.

With these first approaches, we are in conditions to design a 128-points DFT *radix*-2³. Applying the divide and conquer strategy by decomposition of a 128-point DFT in smaller

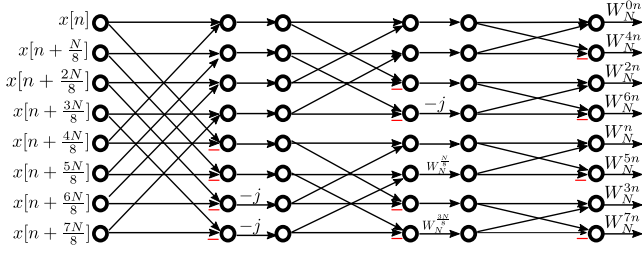
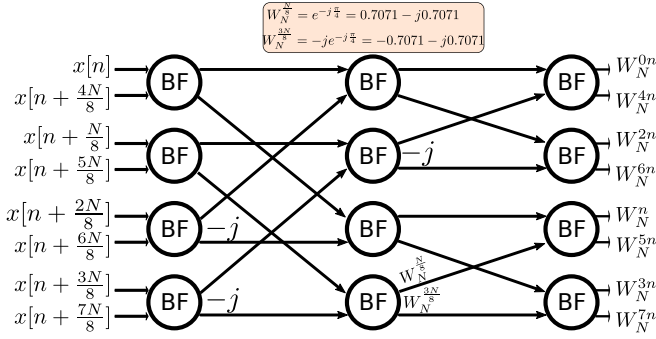
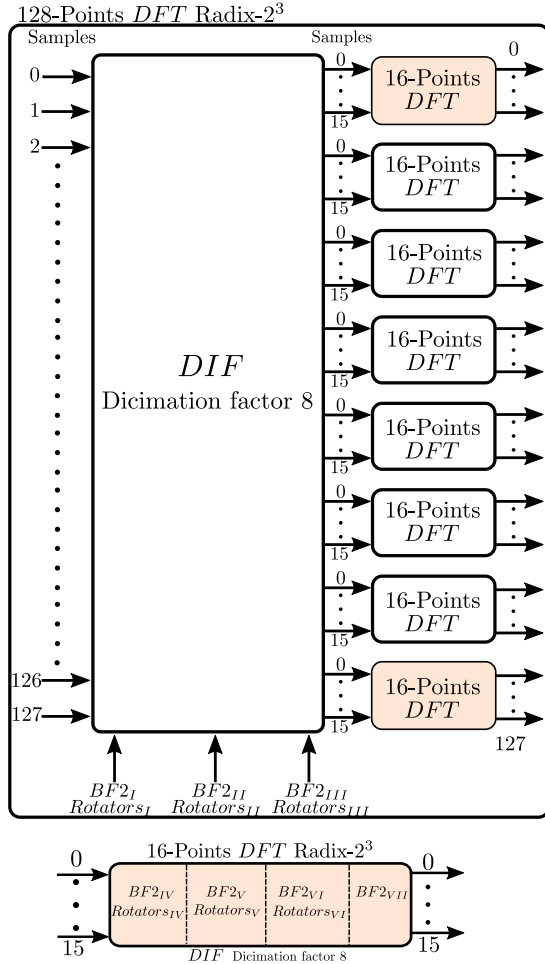
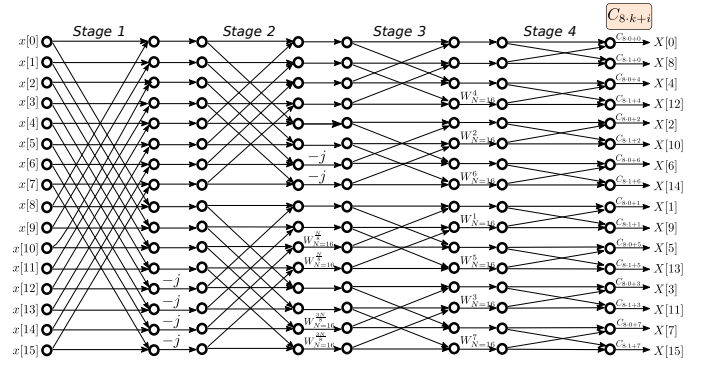
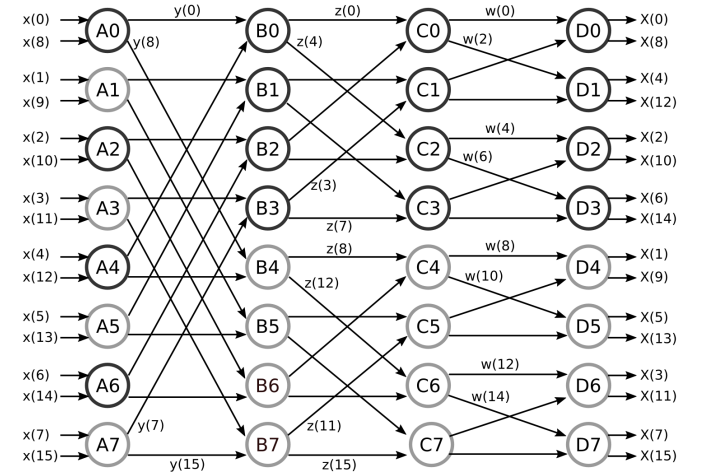
Figure 2: Structure of interconnection for $\text{radix-}2^3$ DIF DFT

Figure 3: Data flow graph (DFG) based in equations (4).

Figure 4: Decomposing a $\text{radix-}2^3$ 128-point DFT

128 point DFT and calculating each coefficient $C_{8k+i} = \sum_{n=0}^{128/8-1} \{\cdot\}$, for $k = 0, 1, \dots, (128/8) - 1$. In this way we get a sequence in chain of butterflies with its corresponding rotation factor and the correct index of the samples in which they must be added or multiplied. This technique lets us do a subdivision on butterflies' stages, in Fig. 4 we can see that the 128 point DFT goes through a process that involves three stages of butterflies to arrive finally to a set of eight DFT where each of them is a 16 point DFT.

The next step to calculate finally our 128 point DFT is to find the suitable rotator factors for the 16 point DFT, this process follows exactly the same calculation that we commented previously, the use of the above equations (4) are essential for this design and they are evaluated to get $C_{8k+i} = \sum_{n=0}^{16/8-1} \{\cdot\}$, for $k = 0, 1$. The structure for the 16 point DFT is described in Fig. 5 and Fig. 6.

Figure 5: Flow graph of a $\text{radix-}2^3$ 16-point DIF DFTFigure 6: Data flow graph (DFG) for a $\text{radix-}2^3$ 16-point DIF DFT

With the DFT's previous decomposition we learned how to get all the coefficients C_{8k+i} that represent the samples in frequency $X[k]$ obtained from a combination of the different instances of $x[n]$. This method takes us to apply step by step the equation (4) to our design and finally arrive to the definitive architecture, the Fig. 7 shows us a $\text{radix-}2^3$ 128-point DIF DFT with a total of seven stages where each stage is building with 64 butterflies of radix-2 base.

DFTs. We begin to apply the set of equations (4) for the

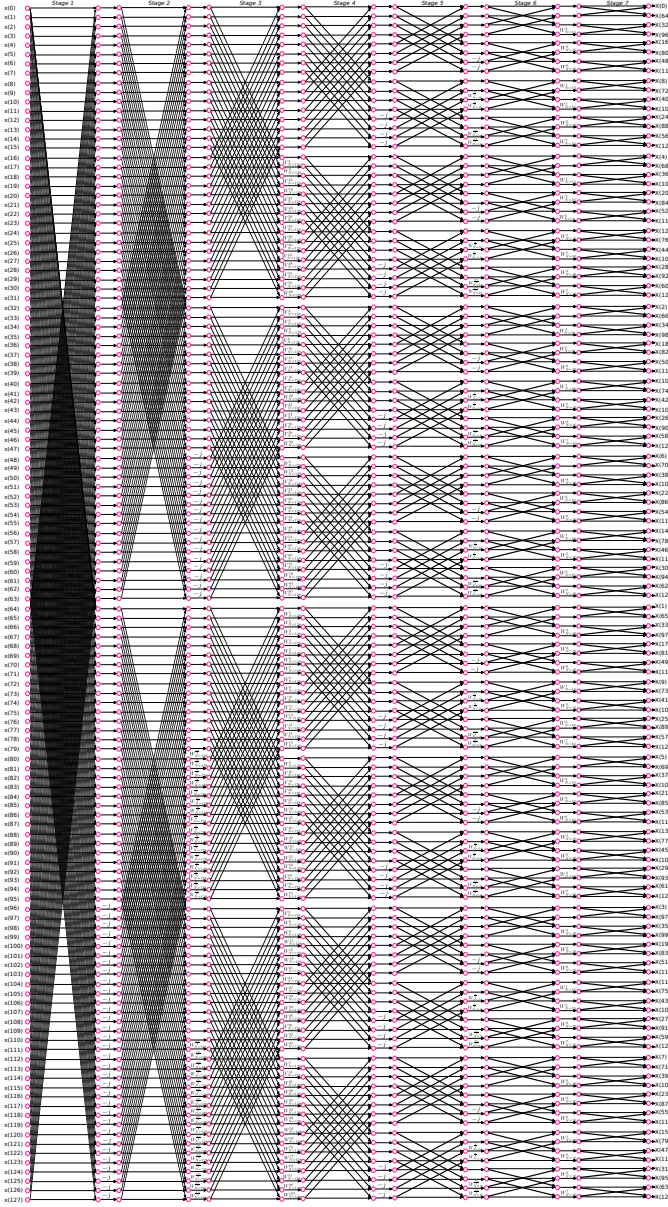


Figure 7: Flow graph of a $\text{radix-}2^3$ 128-point DIF DFT

III. DESIGN OF FFT ARCHITECTURE VIA FOLDING TRANSFORMATION

In this section, we illustrate the folding transformation method to derive a 16-point DIF FFT 4-parallel architecture as an example and then, using the same method, we extend it to 128-point architecture. To do this, we will use the architecture proposed in [5], to do the folding transformation and register minimization techniques we will use [6].

A. 4-Parallel $\text{radix-}2^3$ 16-Points

In Fig. 5 we can see the flow graph of a 16-point DIF FFT $\text{radix-}2^3$ with main base $\text{radix-}2$. The graph is divided into four stages and each of them consist of a set of butterflies and multipliers. The twiddle factor in between the stages indicates a multiplication by W_N^k , where W_N denotes the N th root of unity, with its exponent evaluated modulo N . This

can be represented as a DFG as shown in Fig. 6 where the nodes represents the butterfly computations of the $\text{radix-}2$ FFT algorithm.

The folding transformation is used on the DFG to derive a pipelined architecture. To do this we need a folding set, which is an ordered set of operations executed by the same functional unit. Each folding set contains K entries, where K is called the folding factor. The operation in the j th position within the folding set (where goes from 0 to $K-1$) is executed by the functional unit during the time partition, this term is called the folding order.

First we need to derive the folding equations, to do this consider an edge e connecting the nodes U and V with $w(e)$ delays. Let the executions of the l th iteration of the nodes U and V be scheduled at the time units $Kl + u$ and $Kl + v$ respectively, where u and v are the folding orders of the nodes U and V , respectively. The folding equation for the edge e is:

$$D_F(U \rightarrow V) = Kw(e) - P_U + v - u \quad (5)$$

where P_U is the number of pipeline stages in the hardware unit which executes the node U .

Consider folding of the the DFG in Fig. 6 with the folding sets:

$$\begin{aligned} A &= \{A0, A2, A4, A6\} & A' &= \{A1, A3, A5, A7\} \\ B &= \{B1, B3, B5, B7\} & B' &= \{B2, B4, B6, B8\} \\ C &= \{C2, C1, C3, C0\} & C' &= \{C6, C5, C7, C4\} \\ D &= \{D3, D0, D2, D1\} & D' &= \{D7, D4, D6, D5\} \end{aligned}$$

Assuming that the butterfly operations do not have any pipeline stages ($P_A = P_B = P_C = P_D = 0$), the folding equations can be derived for all edges. Thus, we can obtained from (5) the expressions *without apply retiming*.

$$\begin{aligned} D_F(D0 \rightarrow B0) &= 2 & D_F(D0 \rightarrow B4) &= 2 \\ D_F(D1 \rightarrow B1) &= 0 & D_F(D1 \rightarrow B5) &= 0 \\ D_F(D2 \rightarrow B2) &= 2 & D_F(D2 \rightarrow B6) &= 2 \\ D_F(D3 \rightarrow B3) &= -1 & D_F(D3 \rightarrow B7) &= -1 \\ D_F(D4 \rightarrow B0) &= 0 & D_F(D4 \rightarrow B4) &= 0 \\ D_F(D5 \rightarrow B1) &= -1 & D_F(D5 \rightarrow B5) &= -1 \\ D_F(D6 \rightarrow B2) &= 0 & D_F(D6 \rightarrow B6) &= 0 \\ D_F(D7 \rightarrow B3) &= -2 & D_F(D7 \rightarrow B7) &= -2 \\ D_F(E0 \rightarrow C0) &= 1 & D_F(E0 \rightarrow C2) &= -2 \\ D_F(E1 \rightarrow C1) &= 1 & D_F(E1 \rightarrow C3) &= 2 \\ D_F(E2 \rightarrow C0) &= 0 & D_F(E2 \rightarrow C2) &= -3 \\ D_F(E3 \rightarrow C1) &= 0 & D_F(E3 \rightarrow C3) &= 1 \\ D_F(E4 \rightarrow C4) &= 1 & D_F(E4 \rightarrow C6) &= -2 \\ D_F(E5 \rightarrow C5) &= 1 & D_F(E5 \rightarrow C7) &= 2 \\ D_F(E6 \rightarrow C4) &= 0 & D_F(E6 \rightarrow C6) &= -3 \\ D_F(E7 \rightarrow C5) &= 0 & D_F(E7 \rightarrow C7) &= 1 \\ D_F(F0 \rightarrow D0) &= -2 & D_F(F0 \rightarrow D1) &= 0 \\ D_F(F1 \rightarrow D0) &= 0 & D_F(F1 \rightarrow D1) &= 2 \\ D_F(F2 \rightarrow D2) &= 2 & D_F(F2 \rightarrow D3) &= 0 \\ D_F(F3 \rightarrow D2) &= 0 & D_F(F3 \rightarrow D3) &= -2 \\ D_F(F4 \rightarrow D4) &= -2 & D_F(F4 \rightarrow D5) &= 0 \\ D_F(F5 \rightarrow D4) &= 0 & D_F(F5 \rightarrow D5) &= 2 \\ D_F(F6 \rightarrow D6) &= 2 & D_F(F6 \rightarrow D7) &= 0 \\ D_F(F7 \rightarrow D6) &= 0 & D_F(F7 \rightarrow D7) &= -2 \end{aligned}$$

For the folded system to be realizable, $D_F(U \rightarrow V) \geq 0$ must hold for all the edges in the DFG. Retiming and/or pipeline can be applied to satisfy this property, if the DFG in Fig. 6 is pipelined/retimed as shown in Fig. 8 the system is realizable and the folded delays for the edges are given by the equations that represent a folding set *with retiming*

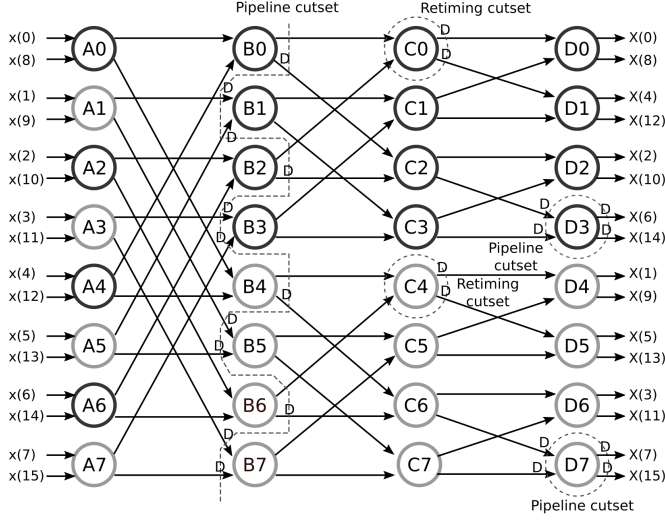


Figure 8: Data Flow graph (DFG) of a radix-2 16-point DIF FFT with retiming and pipeline.

$$\begin{aligned}
 D_F(D0 \rightarrow B0) &= 2 & D_F(D0 \rightarrow B4) &= 2 \\
 D_F(D1 \rightarrow B1) &= 4 & D_F(D1 \rightarrow B5) &= 4 \\
 D_F(D2 \rightarrow B2) &= 2 & D_F(D2 \rightarrow B6) &= 2 \\
 D_F(D3 \rightarrow B3) &= 3 & D_F(D3 \rightarrow B7) &= 3 \\
 D_F(D4 \rightarrow B0) &= 0 & D_F(D4 \rightarrow B4) &= 0 \\
 D_F(D5 \rightarrow B1) &= 3 & D_F(D5 \rightarrow B5) &= 3 \\
 D_F(D6 \rightarrow B2) &= 0 & D_F(D6 \rightarrow B6) &= 0 \\
 D_F(D7 \rightarrow B3) &= 2 & D_F(D7 \rightarrow B7) &= 2 \\
 D_F(E0 \rightarrow C0) &= 1 & D_F(E0 \rightarrow C2) &= 2 \\
 D_F(E1 \rightarrow C1) &= 1 & D_F(E1 \rightarrow C3) &= 2 \\
 D_F(E2 \rightarrow C0) &= 0 & D_F(E2 \rightarrow C2) &= 1 \\
 D_F(E3 \rightarrow C1) &= 0 & D_F(E3 \rightarrow C3) &= 1 \\
 D_F(E4 \rightarrow C4) &= 1 & D_F(E4 \rightarrow C6) &= 2 \\
 D_F(E5 \rightarrow C5) &= 1 & D_F(E5 \rightarrow C7) &= 2 \\
 D_F(E6 \rightarrow C4) &= 0 & D_F(E6 \rightarrow C6) &= 1 \\
 D_F(E7 \rightarrow C5) &= 0 & D_F(E7 \rightarrow C7) &= 1 \\
 D_F(F0 \rightarrow D0) &= 2 & D_F(F0 \rightarrow D1) &= 4 \\
 D_F(F1 \rightarrow D0) &= 0 & D_F(F1 \rightarrow D1) &= 2 \\
 D_F(F2 \rightarrow D2) &= 2 & D_F(F2 \rightarrow D3) &= 4 \\
 D_F(F3 \rightarrow D2) &= 0 & D_F(F3 \rightarrow D3) &= 2 \\
 D_F(F4 \rightarrow D4) &= 2 & D_F(F4 \rightarrow D5) &= 4 \\
 D_F(F5 \rightarrow D4) &= 0 & D_F(F5 \rightarrow D5) &= 2 \\
 D_F(F6 \rightarrow D6) &= 2 & D_F(F6 \rightarrow D7) &= 4 \\
 D_F(F7 \rightarrow D6) &= 0 & D_F(F7 \rightarrow D7) &= 2
 \end{aligned} \tag{6}$$

We can see that the number of registers required to implement the folding equations in (6) is 80. For minimize the number of registers we use the register minimization technique. If we let the output of node A0 be $y_{(0)}$ and $y_{(8)}$ and the output of the node A1 be $y_{(1)}$ and $y_{(9)}$, applying this successively with

	I/P	R1	R2	R3	R4	R5	R6	R7	R8
0	$y_{0,y8,y1,y9}$								
1	$y_{2,y10,y3,y11}$	y_1		y_0		y_9		y_8	
2	(y_4,y_{12},y_5,y_{13})	y_3	y_1	y_2	(y_0)	y_{11}	y_9	y_{10}	(y_8)
3	(y_6,y_{14},y_7,y_{15})	y_5	y_3	y_1	(y_2)	y_{13}	y_{11}	y_9	(y_{10})
4		y_7	(y_5)	y_3	(y_1)	y_{15}	y_{13}	y_{11}	(y_9)
5			(y_7)		(y_3)		y_{15}		(y_{11})

Figure 9: Linear lifetime chart for the variables $y_{(0)}, y_{(1)}, \dots, y_{(15)}$ for a 16-point FFT architecture.

	I/P	R1	R2	R3	R4
2	$z_{0,z4,z8,z_{12}}$				
3	$(z_2)z_6(z_{10})z_{14}$	z_4	(z_0)	z_{12}	(z_8)
4	z_1,z_5,z_9,z_{13}	(z_6)	(z_4)	(z_{14})	(z_{12})
5	$(z_3)z_7(z_{11})z_{15}$	z_5	(z_1)	z_{13}	(z_9)
6		(z_7)	(z_5)	(z_{15})	z_{13}

Figure 10: Linear lifetime chart for the variables $z_{(0)}, z_{(1)}, \dots, z_{(15)}$ for a 16-point FFT architecture.

	I/P	R1	R2	R3	R4	R5	R6	R7	R8
4	$w_{0,w2,w8,w_{10}}$								
5	$w_{4,w6,w_{12},w_{14}}$	w_2		w_0		w_{10}		w_8	
6	$(w_1)w_3(w_9)w_{11}$	w_6	w_2	w_4	(w_0)	w_{14}	w_{10}	w_{12}	(w_8)
7	$(w_5)w_7(w_{13})w_{15}$	w_3	w_6	w_2	(w_4)	w_{11}	w_{14}	w_{10}	(w_{12})
8		w_7	(w_3)	w_6	(w_2)	w_{15}	(w_{11})	w_{14}	(w_{10})
9			(w_7)		(w_6)		(w_{15})		(w_{14})

Figure 11: Linear lifetime chart for the variables $w_{(0)}, w_{(1)}, \dots, w_{(15)}$ for a 16-point FFT architecture.

the rest of the nodes A we can obtain the linear life time chart for this stage in Fig. 9. Applying this criteria to the rest of the stages we can obtain the life time chart 10 and 11 for the outputs of the nodes B and C respectively, we can see that the numbers of maximum registers in each stage are 8, 4 and 8 respectively. More information about this method can be found on [6]. The register allocation tables for each of lifetime charts are shown in Fig. 12, 13 and 14 respectively, we can implement the same equations in (6) using 20 registers with register minimization techniques. The folded architecture in Fig. 17 is synthesized using the folding equations and the register allocation tables, the method can be found on [6].

The inputs of each folding node are represented with a matrix where the values in the same column are data that flow

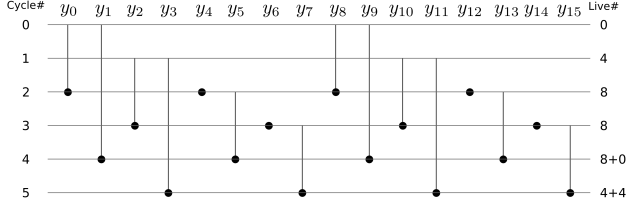


Figure 12: Register allocation table for the data represented in 9

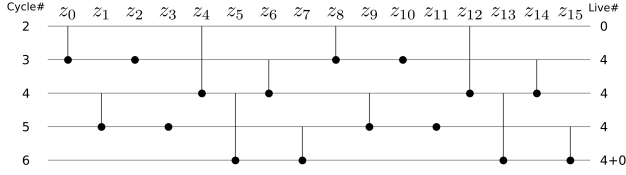


Figure 13: Register allocation table for the data represented in 10

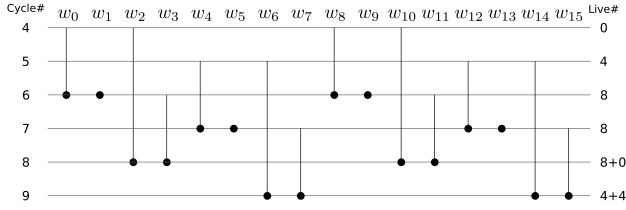


Figure 14: Register allocation table for the data represented in 11

in parallel and values in the same row flow through the same path in consecutive clock cycles. The first two rows represents the inputs of the superior BF and the others two represents the input of the inferior BF. The same criteria is used for represent the constants of rotators, where each number k of the matrix represent a multiplication by W_N^k .

As we can see in Fig. 17, we suppose that the inputs and output are not ordered, to order these variables extra logic are needed, using more registers and multiplexers.

The different types of rotators used in Fig. 17 are shown in Fig. 15, the description of each of them can be found below.

- Trivial rotator: They can be carried out by interchanging the real and imaginary components and/or changing the sign of the data.
- Constant CSD rotator: They can be carried out by interchanging the real and imaginary components and a multiplication by a unique constant fractional number, in this case we will use a CSD multiplier to perform the area utilized.
- General rotator: They can be carried out by interchanging the real and imaginary components and/or a multiplication by more than one constant fractional numbers, in this case we will use a general multiplier.

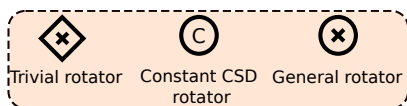


Figure 15: Symbols used for the different types of rotators

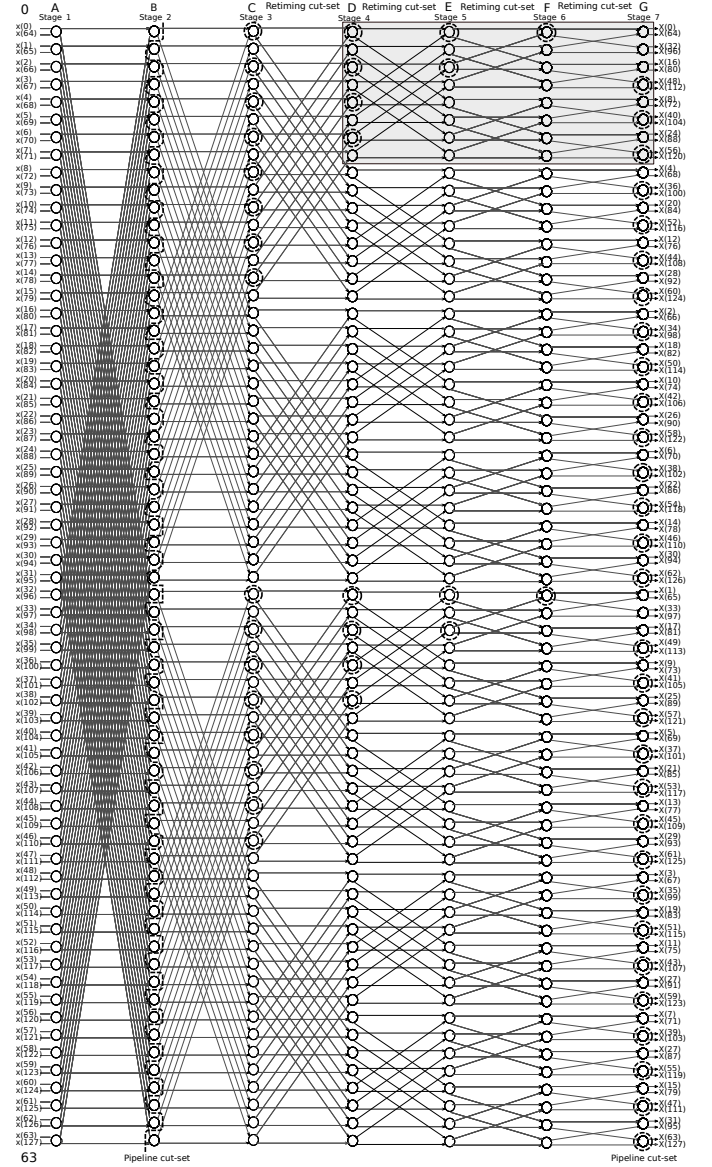


Figure 16: Pipelined DFG of a 128-point DIF FFT as a preprocessing step for folding.

B. 4-Parallel radix-2³ 128-Points

We can deduce the folding architecture for 128 points following the same method than used with the 4-Parallel radix-2³ 16-Points. The DFG and folding set used can be shown in Fig. 16 and Table I. The architecture can be seen in Fig. 18.

IV. IMPLEMENTATION

In this section we are going to begin with the process of how accomplish the implementation of our 4-parallel architecture for the computation of 128-point radix-2³ DIF complex FFT. First, we wrote a *MATLAB* simulator to validate the operation of our design and the design presented in [7], [8]. Therefore, we can have a reference architecture for compare the design that we deduce. After that, we take all these information to generate a Synthesizable *Verilog* code with different levels of

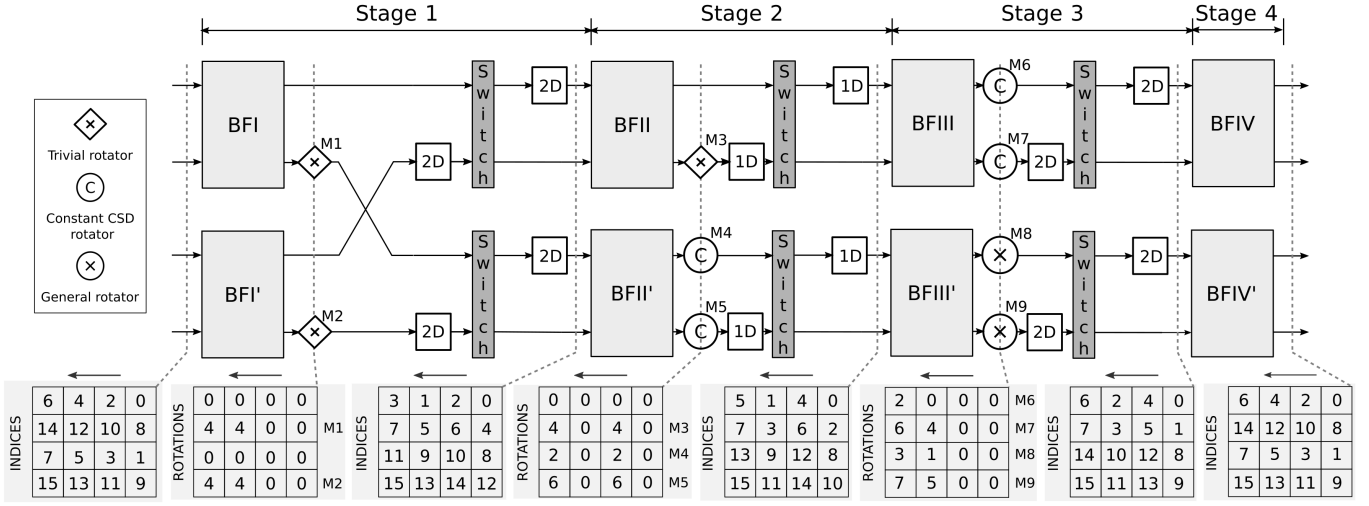


Figure 17: Folding architecture for the computation of a radix- 2^3 16-point DIF complex FFT.

Table I: Folding set for the DFG showed in Fig. 16

A	A0	A2	A4	A6	A8	A10	A12	A14	A16	A18	A20	A22	A24	A26	A28	A30
A'	A32	A34	A36	A38	A40	A42	A44	A46	A48	A50	A52	A54	A56	A58	A60	A62
B	B1	B3	B5	B7	B9	B11	B13	B15	B17	B19	B21	B23	B25	B27	B29	B31
B'	B0	B2	B4	B6	B8	B10	B12	B14	B16	B18	B20	B22	B24	B26	B28	B30
C	B33	B35	B37	B39	B41	B43	B45	B47	B49	B51	B53	B55	B57	B59	B61	B63
C'	B32	B34	B36	B38	B40	B42	B44	B46	B48	B50	B52	B54	B56	B58	B60	B62
D	C16	C18	C20	C22	C24	C26	C28	C30	C1	C3	C5	C7	C9	C11	C13	C15
D'	C17	C19	C21	C23	C25	C27	C29	C31	C0	C2	C4	C6	C8	C10	C12	C14
E	C48	C50	C52	C54	C56	C58	C60	C62	C33	C35	C37	C39	C41	C43	C45	C47
E'	C49	C51	C53	C55	C57	C59	C61	C63	C32	C34	C36	C38	C40	C42	C44	C46
F	D8	D10	D12	D14	D16	D18	D20	D22	D24	D26	D28	D30	D1	D3	D5	D7
F'	D9	D11	D13	D15	D17	D19	D21	D23	D25	D27	D29	D31	D0	D2	D4	D6
G	D40	D42	D44	D46	D48	D50	D52	D54	D56	D58	D60	D62	D33	D35	D37	D39
G'	D41	D43	D45	D47	D49	D51	D53	D55	D57	D59	D61	D63	D32	D34	D36	D38
H	E4	E6	E8	E10	E12	E14	E16	E18	E20	E22	E24	E26	E28	E30	E1	E3
H'	E5	E7	E9	E11	E13	E15	E17	E19	E21	E23	E25	E27	E29	E31	E0	E2
I	E36	E38	E40	E42	E44	E46	E48	E50	E52	E54	E56	E58	E60	E62	E33	E35
I'	E37	E39	E41	E43	E45	E47	E49	E51	E53	E55	E57	E59	E61	E63	E32	E34
J	F2	F4	F6	F8	F10	F12	F14	F16	F18	F20	F22	F24	F26	F28	F30	F1
J'	F3	F5	F7	F9	F11	F13	F15	F17	F19	F21	F23	F25	F27	F29	F31	F0
K	F34	F36	F38	F40	F42	F44	F46	F48	F50	F52	F54	F56	F58	F60	F62	F33
K'	F35	F37	F39	F41	F43	F45	F47	F49	F51	F53	F55	F57	F59	F61	F63	F32
L	G3	G5	G7	G9	G11	G13	G15	G17	G19	G21	G23	G25	G27	G29	G31	G0
L'	G2	G4	G6	G8	G10	G12	G14	G16	G18	G20	G22	G24	G26	G28	G30	G1
M	G35	G37	G39	G41	G43	G45	G47	G49	G51	G53	G55	G57	G59	G61	G63	G32
M'	G34	G36	G38	G40	G42	G44	G46	G48	G50	G52	G54	G56	G58	G60	G62	G33

optimizations with a powerful tool like *Synopsys* to get a final design integrated of Standard Cells @45nm.

A. Floating and Fixed point Simulator

The input signal Fig. 20 to our architecture will be a mixture of sinusoid signals with two frequency values, these signal will be normalizing to the unity and in this way we can have a test bench design.

$$\begin{aligned} x'[n] &= \cos(2\pi f_1 n T_s) + \cos(2\pi f_2 n T_s) \\ x[n] &= x'[n] / \max\{x'[n]\} \end{aligned} \quad (7)$$

where $f_1 = 100Hz$, $f_2 = 1000Hz$ and T_s is the sampled period.

In each stage of the Fig. 19, input samples that propagate stage by stage will be carefully quantized with the purpose of getting a high SQNR (Signal to Quantization Noise Ratio).

$$SQNR_{dB} = 10 \log_{10} \left(\frac{Var\{Signal_{FloatPoint}\}}{Var\{Signal_{FloatPoint} - Signal_{FixedPoint}\}} \right)$$

SQNR computation represents the logarithmic relationship between float signal variance over error variance from an signal given.

The input signal $x[n]$ is quantized with a value of $S(10, 9)$, that representation means a number signed (S) with 10 total bits and 9 fractional bits. The value calculated of SQNR for the input is 56.9dB. Following the same steps, we can compute the SQNR for the *twiddle* factors and the architecture's output.

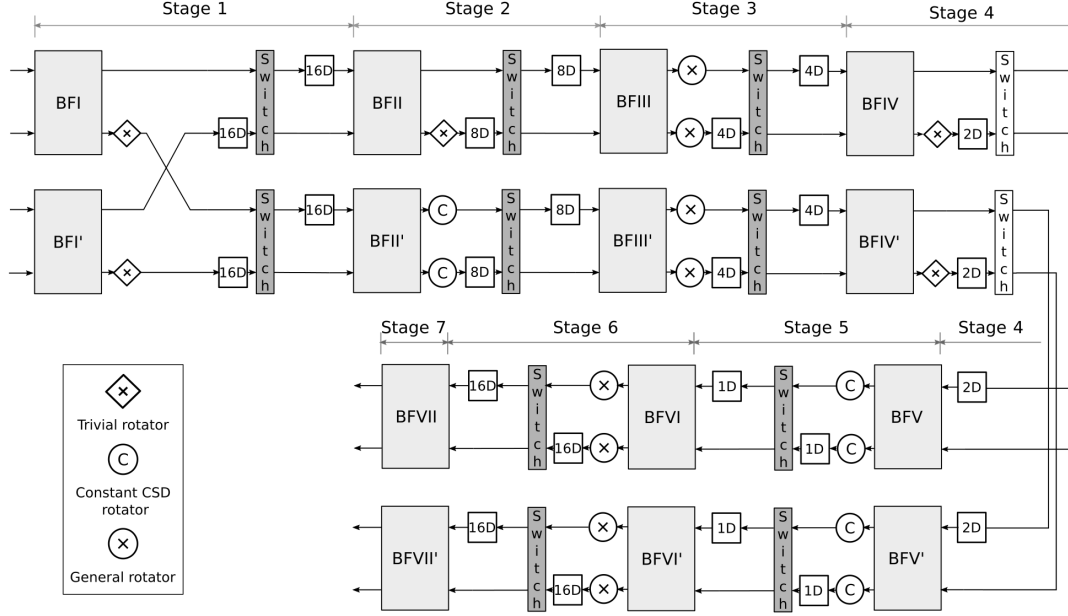


Figure 18: Folding architecture for the computation of a radix- 2^3 128-point DIF complex FFT.

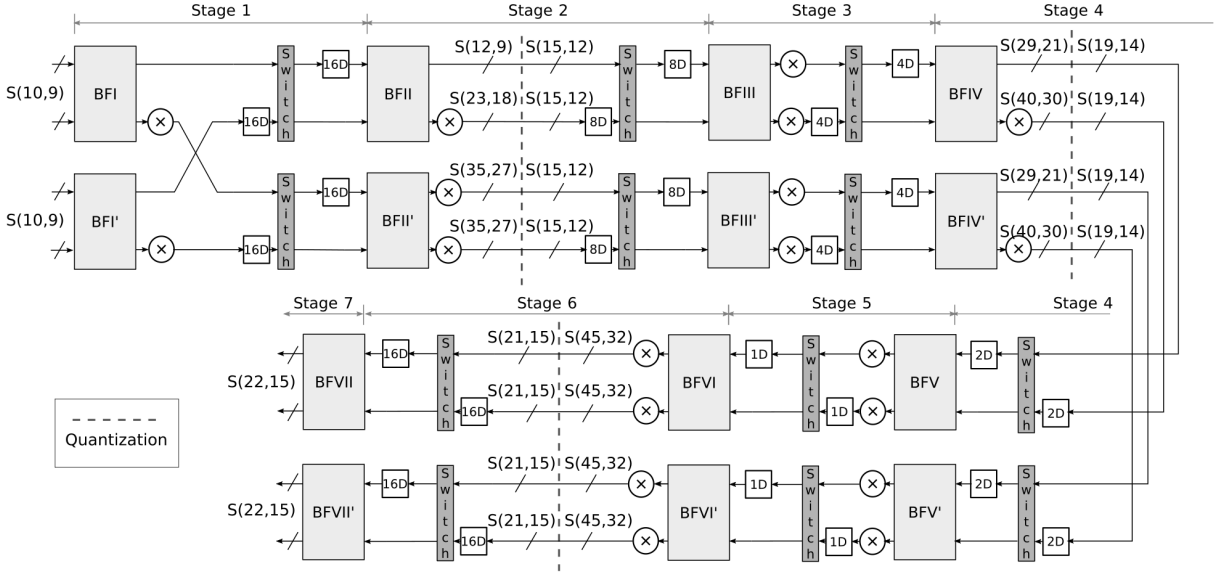


Figure 19: Quantization for a 128-point 4-parallel complex FFT architecture

Twiddle factors are quantized with a relation of $S(11,9)$ and the complex output signal $X[k]$ with $S(22,15)$. Output quantization for the real part is 46.8dB and for the imaginary part 47.3dB. In general, a value of quantization close to 50dB is a good approximation. Output signal from our *MATLAB* fixed-point model from the architecture in Fig. 19 the output signal is given in Fig. 21, that represents a first approach in our calculation of a DFT without optimization.

The combination between latencies (delay registers) and switches in all stages in Fig. 19 is the equivalent circuit shown in Fig. 22, that is used to appropriately order samples in each butterfly's input.

Whole elements on the architecture such as multipliers and butterflies are complex as Fig. 23 and 24. On an implementa-

tion is essential to divide the signal in its real and imaginary part with the purpose of processing them independently. A *general rotator* (full complex multiplier) generates a real and imaginary component that is composed by a real multiplication and one addition, but a *trivial rotator* only changes the components of a complex signal. These relations are important at the moment of doing the quantization process to ensure an appropriate quantity of bits.

B. Verilog (HDL) Model

In this subsection we are going to talk about the different design instances to model the DFT in hardware. We made four design implementations with the purpose of having a global view of optimization levels to achieve the requested *Timing* at

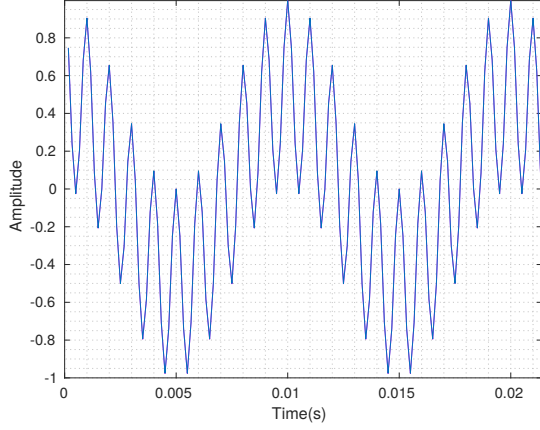
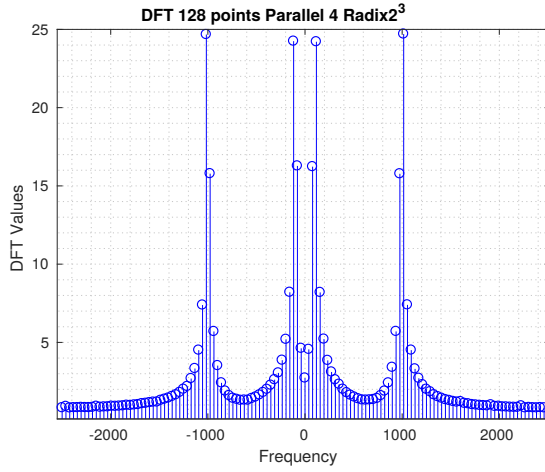
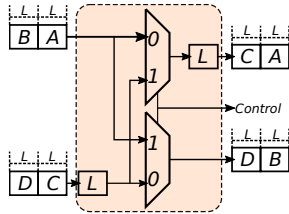
Figure 20: Input signal $x[n]$ in time domainFigure 21: Output samples, absolute value vs frequency $|X[k]|$ 

Figure 22: Circuit for data shuffling

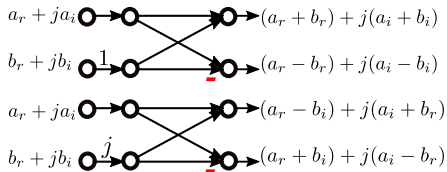


Figure 23: Complex butterfly

a working frequency of 500MHz obtained from the synthesis processes.

In the first instance of design was made from the base design showed in Fig. 19, this hardware model has butterflies modules that work in combination with multipliers and each multiplier has associated a memory block that contains twiddle

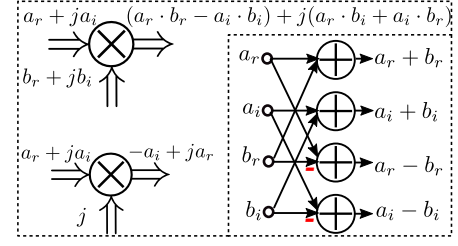


Figure 24: Complex multiplier and complex adder

factors. In this first approach all multipliers are *full*, each stage has a control module that enable and disable the inversion of the switching block, this control signal is also sent to the multipliers to work synchronously with the switching. To avoid the bit growth generated by the addition and multiplication, a quantization block is necessary, the quantizer consisted of saturation and truncate operations.

In the second place with the goal of minimize the *critical path* in our design, we add *pipelined* registers after quantization blocks. In the third case of implementation incorporate *trivial* multipliers, imaginary multiplication by $-1j$, with this kind of operation we can reduce the size of the binary word.

In the fourth level of optimization showed in Fig. 25, we place inside each butterfly blocks an internal pipelined to improve the required timing. Lastly, the full multipliers from stage two and five are modified to efficiently work with constant coefficients, these new multipliers are *CSD* because the twiddle factors in these stages are always $-je^{-j\frac{\pi}{4}}$ and $e^{-j\frac{\pi}{4}}$.

V. RESULTS

All designs were implemented with different levels of optimization to accomplish the desired working frequency. The design instances were synthesized by Synopsys tool in order to build an interconnection of Standard Cells to get and generate a complete set of *timing-area-power report* showed in Table II, III, IV and V. According to the first results, data arrival time is greater than minimum period established 2ns and we can detected that there is a time Violated, with this first approach we decide make a set of optimizations to folding architecture as a pipelined cutset between stages of DFT. In this way as we can see in Table V, we reduced power, area and timing.

In contrast with the first instance of design, we found in the last case of implementation a slack of time equal to zero, that means the clock period satisfy the time constraint at 500MHz.

VI. CONCLUSION

This work has presented a VLSI Implementation of a Pipelined 128 points 4-Parallel radix-2³ FFT Architecture via Folding Transformation. The Fourier Transform without folding technique processes 128 entry points of samples which are ordered but its output are disordered and it is necessary a reordering circuit. In the other hand a Fourier Transform with folding technique also needs a reordering circuit in the input. This circuit present an additional area and power consumption to be considered in the final design.

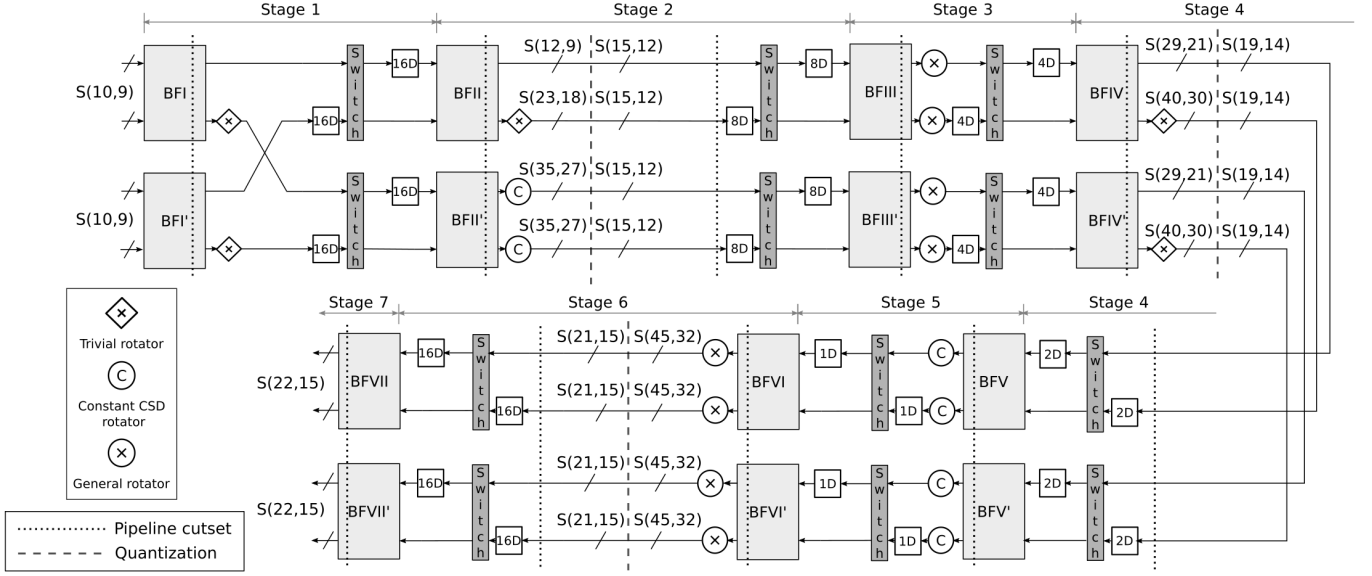


Figure 25: RTL (Register transfer level) design for a 4-parallel $radix-2^3$ 128-point DIF FFT with Optimization

Table II: Design instance 1. Timing-Area-Power Report at 500MHz

Point	Path(ns)
data arrival time	5.60
clock CLK (rise edge)	2.00
clock network delay (ideal)	2.00
library setup time	1.95
data required time	1.95
data arrival time	-5.60
slack (VIOLATED)	-3.65

Logical Elements

Number of ports	1228
Number of nets	112376
Number of cells	102726
Number of combinational cells	95310
Number of sequential cells	7404
Number of macros/black boxes	0
Number of buf/inv	27817
Combinational area	291201.116637
Buf/Inv area	44892.767764
Noncombinational area	58830.508095
Total cell area	350031.624731

Table III: Design instance 2. Timing-Area-Power Report at 500MHz

Point	Path(ns)
data arrival time	2.71
clock CLK (rise edge)	2.00
clock network delay (ideal)	2.00
library setup time	1.95
data required time	1.95
data arrival time	-2.71
slack (VIOLATED)	-0.76

Logical Elements

Number of ports	1826
Number of nets	114367
Number of cells	104198
Number of combinational cells	96271
Number of sequential cells	7912
Number of macros/black boxes	0
Number of buf/inv	26770
Combinational area	294733.068172
Buf/Inv area	41738.133324
Noncombinational area	62955.185703
Total cell area	357688.253875

Power Group	Internal	Switching	Leakage	Total Power
io pad	0.0000	0.0000	0.0000	0.0000
clock network	34.8220	603.2268	1.4573e+06	639.6328
register	54.2228	0.2699	4.0540e+05	54.8980
sequential	0.0000	0.0000	0.0000	0.0000
combinational	0.2884	0.7304	1.5016e+04	1.0337
Total	89.333mW	604.227mW	1.877e+06nW	695.564mW

Power Group	Internal	Switching	Leakage	Total Power
io pad	0.0000	0.0000	0.0000	0.0000
clock network	36.5175	603.3234	1.3702e+06	641.2228
register	57.8422	0.2604	4.3383e+05	58.5363
sequential	0.0000	0.0000	0.0000	0.0000
combinational	0.5748	1.4180	1.5702e+05	2.1498
Total	94.934mW	605.001mW	1.961e+06nW	701.908mW

The folding transformation applied reduce significantly (equal to the folded factor, i.e. 64 times) the number of functional units, and therefore the silicon area, at the expense of increasing the computation time by the same factor. Therefore is necessary to add pipelined cutsets and a careful quantization in order to achieve the required sample period with an acceptable SNR.

Folding technique, in this case, results in an architecture that uses a large number of register, to avoid this is necessary to apply a register minimization technique and allocate data to

these registers. The number of registers applying this method is reduced significantly, from to . This results in a final design with less area and power consumption.

The number of DFT points is related with the radix-base, we can write as $radix-8$, this representation can be expressed as $radix-2^3$ that means we can decompose in smaller radices with main base-2, an advantage of using a high radix is reduced the number of multipliers at expense of increase the routing.

Our design has implemented a quantizer block which works with saturation and truncated, the round method was not

Table IV: Design instance 3. Timing-Area-Power Report at 500MHz

Point	Path(ns)
data arrival time	2.76
clock CLK (rise edge)	2.00
clock network delay (ideal)	2.00
library setup time	1.95
data required time	1.95
data arrival time	-2.76
slack (VIOLATED)	-0.81

Logical Elements	
Number of ports	1571
Number of nets	94523
Number of cells	87311
Number of combinational cells	80220
Number of sequential cells	7076
Number of macros/black boxes	0
Number of buf/inv	23823
Combinational area	233949.801414
Buf/Inv area	36323.350042
Noncombinational area	56229.647552
Total cell area	290179.448967

Power Group	Internal	Switching	Leakage	Total Power
io pad	0.0000	0.0000	0.0000	0.0000
clock network	24.2875	583.5885	1.0269e+06	608.9492
register	51.0349	0.1728	3.8748e+05	51.5952
sequential	0.0000	0.0000	0.0000	0.0000
combinational	0.9554	1.1271	1.8640e+05	2.2689
Total	76.277mW	584.888mW	1.600e+06nW	662.813mW

Table V: Design instance 4. Timing-Area-Power Report at 500MHz

Point	Path(ns)
data arrival time	1.94
clock CLK (rise edge)	2.00
clock network delay (ideal)	2.00
library setup time	1.94
data required time	1.94
data arrival time	-1.94
slack (MET)	0.00

Logical Elements	
Number of ports	2315
Number of nets	75713
Number of cells	66284
Number of combinational cells	58017
Number of sequential cells	8240
Number of macros/black boxes	0
Number of buf/inv	14789
Combinational area	195877.841872
Buf/Inv area	24429.880240
Noncombinational area	64463.046570
Total cell area	260340.888442

Power Group	Internal	Switching	Leakage	Total Power
io pad	0.0000	0.0000	0.0000	0.0000
clock network	18.1655	581.6307	7.8320e+05	600.6672
register	58.2275	0.2873	4.4422e+05	58.9591
sequential	0.0000	0.0000	0.0000	0.0000
combinational	0.7768	0.9958	1.5970e+05	1.9322
Total	77.169mW	582.913mW	1.387e+06nW	661.558mW

used because we reached a high SQNR. Lastly a series of optimization were necessary to accomplish the required frequency. The DFT implementation without any optimization level got to work at 166MHz, applying pipelines cutsets and quantization blocks, the final architecture is implementable at the required clock frequency (500 MHz) at the cost of incrementing the numbers of sequential cells. Finally, with the

CSD multipliers, is possible to reduce the combinational cells significantly.

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