

# Praktikum Hochfrequenz-Schaltungstechnik WS25/26

## Bericht

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### 1.5.1

In this section a low-pass filter, like displayed in figure 1, was simulated with *LTspice* [1] for different frequencies via AC-analysis. The result is shown in figure 2.

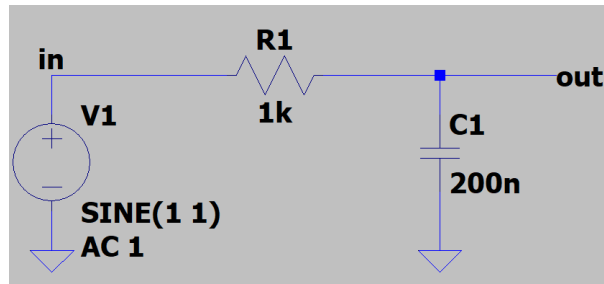


Figure 1: RC-low-pass modeled with *LTspice*

The cutoff frequency  $f_c \approx 795.6$  Hz can be determined at  $-3$  db of the trace. This result compares within 0.17 Hz with the theoretical value acquired through the relation

$$f_c = \frac{1}{2\pi RC} = 795.77 \text{ Hz} \quad (1)$$

between the cutoff frequency  $f_c$ , the resistance  $R = 1 \text{ k}\Omega$  and capacitance  $C = 200 \text{ nF}$  [2]. Further the slope of the voltage trace is measured at  $-5.97$  db/octave ( $-19.95$  db/decade) which fits within 0.03 db/decade of the literature value for first order dampers of  $-20$  db/decade [2].

### 1.5.2

The ratio between input and output voltage at  $f_c$  is characterized as

$$\frac{V_2}{V_1} = \frac{1}{\sqrt{2}} \quad (2)$$

which equals to  $-3$  db [2].

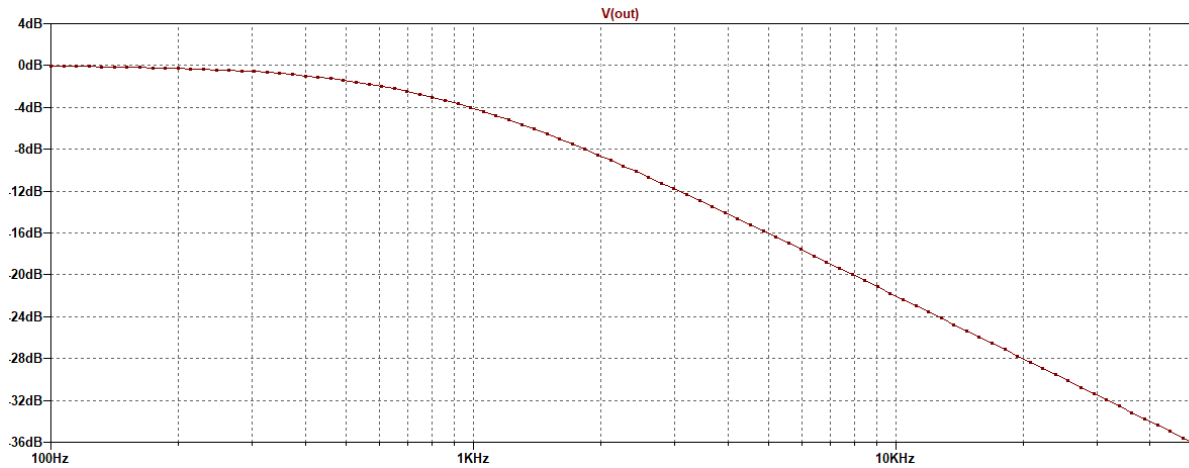


Figure 2: Bode diagram of RC-low-pass shown in fig. 1

### 1.5.3

The voltage source  $V3$  is needed to control the current source  $F1$  with an amplification factor of 200 or 190. It is set at  $0.707\text{ V} \approx 1/\sqrt{2}\text{ V}$  modeling the state at cutoff frequency of a RC-low-pass circuit.

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### 1.5.4

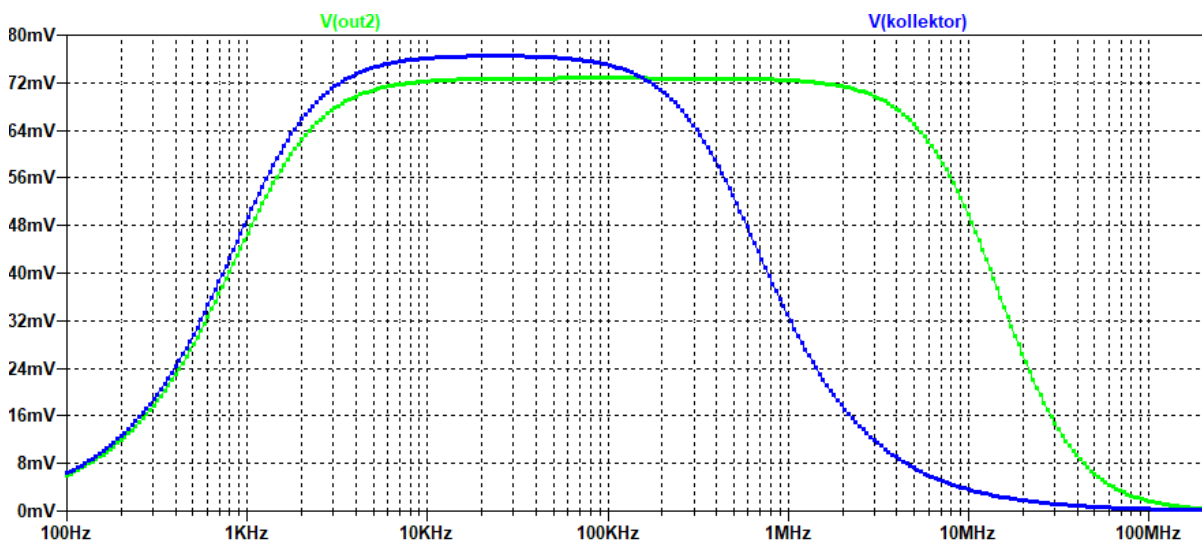


Figure 3: Two frequency responses from the given circuits [?].  $V(\text{out2})$  marks the kaskode circuit and  $V(\text{kollektor})$  the emitter circuit.

### 1.5.5

Comparing the frequency responses of the transistor circuit and voltage control circuit there are many similarities, such as the lower cutoff frequency, their saturation amplification as well as their trajectory in lower frequencies. On the other hand the transis-

tor circuit bears a higher second cutoff frequency at  $f_{c,\text{transistor}} \approx 850 \text{ kHz}$  compared to  $f_c \approx 795.6 \text{ kHz}$  of the voltage controlled circuit.

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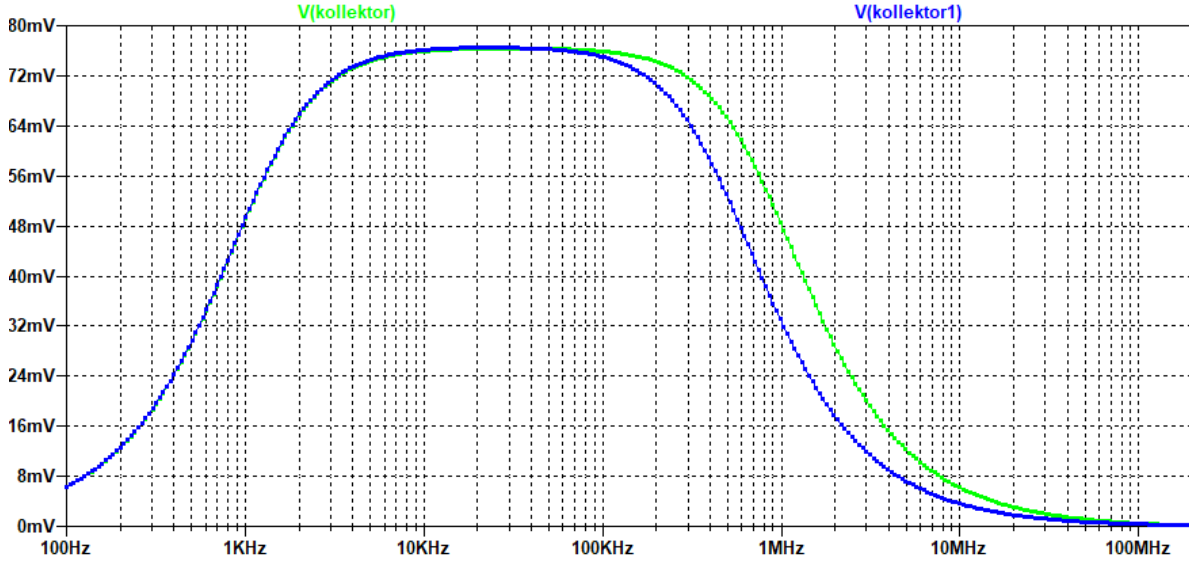


Figure 4: Two frequency responses from the given circuits [?]. V(kollektor) marks the circuit with transistors and V(kollektor1) the voltage controlled circuit.

### 1.5.6

The *Miller Effect* is introduced at an ideal operational amplifier with a finite gain  $v$  with a feedback impedance  $Z_k$ . Under open-circuit output conditions the equivalent input impedance

$$Z_e = \frac{Z_k}{1 - v} \quad (3)$$

appears to be dynamically reduced by the factor  $1 - v$ . If  $Z_k = \frac{1}{j\omega C_k}$  the equivalent input capacitance as shown in figure 5 is enlarged by the same factor – the *Miller Effect*.

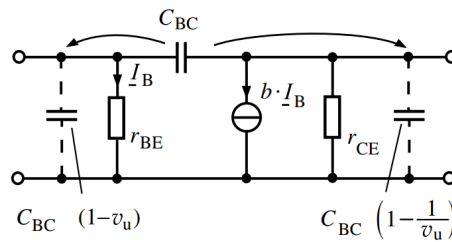


Figure 5: *Miller Effect* in an emitter circuit [2]

In the lab experiment the capacitor  $C_3$  is the *Miller*-capacitor which was varied in this section to achieve similar frequency response properties as with the kaskode circuit. Therefore, its value was altered for each trace V(kollektor) of figure 6. With a capacitance of  $C_3 \approx 200 \text{ fF}$  a similar cutoff frequency to the kaskode circuit can be modeled. varying the capacitor  $C_4$  only increases the descend of the frequency response.

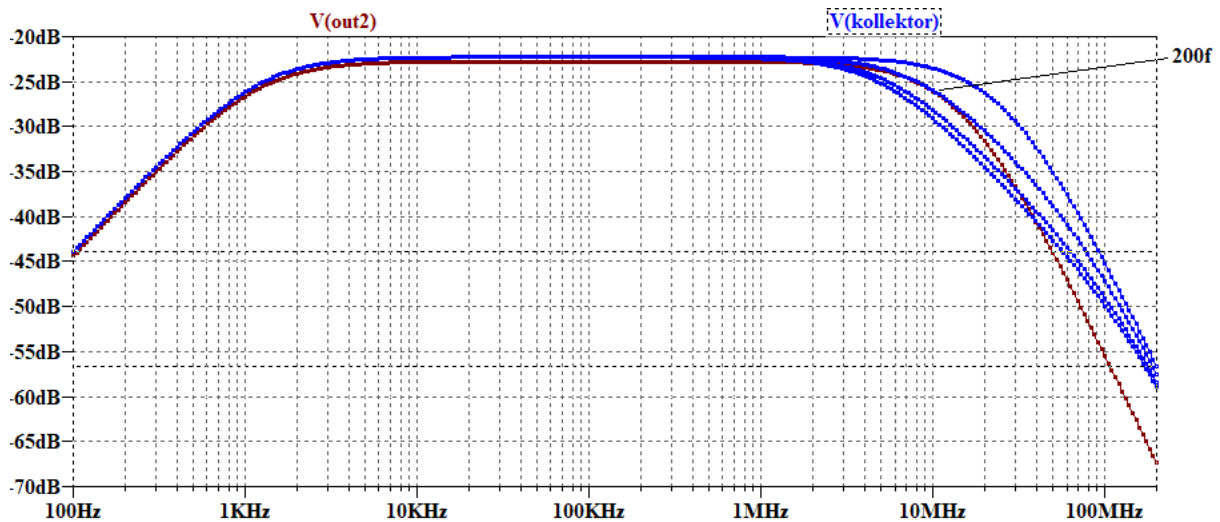


Figure 6: Two frequency responses of the given circuits [?].  $V(out2)$  marks the kaskode circuit and  $V(kollektor)$  displayed frequency responses for varying capacities of the Miller-capacitor from 0 fF up to 500 fF. The marked trace being at 200 fF.

### 1.5.7

Considering the data sheet of a 2N2222 transistor [3] the Output capacitance parameter  $C_{obo} = 8 \text{ pF}$  which is measured at  $V_{CB}$  can be used for  $C3$  since this capacitance is between collector and base of the circuit.  $C4$  is at the emitter of the given circuit and connects to ground and can be modeled with the  $C_{ibo} = 25 \text{ pF}$  parameter of the sheet since this is the base-emitter capacitance (measured with  $V_{EB}$ ) [3]. In our case the base-ground connection resembles a base-emitter connection.

### 1.5.8

The voltage of the source  $V3$  which acts as a current sensor has a value of  $\neq 0$ . This is because the difference in potential of  $0.707 \text{ V}$  is needed to support the given current through the serial resistance of  $806 \Omega$ . It is a 'metric' for the current passing through the resistance.

### 1.5.9

Furthermore, the internal resistance of the source  $V3$  is needed to calculate the potential discussed before. It models the real internal resistance of a measurement tool, which provides numerical stability avoiding short circuits.

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1.5.14

## References

- [1] Ltspice. <https://www.analog.com/en/design-center/design-tools-and-calculators/ltspice-simulator.html>. Accessed: 2025-11-11.
- [2] W. Reinhold. *Elektronische Schaltungstechnik*. Hanser Verlag, München, 4., aktualisierte auflage edition, 2023. Kostenlos verfügbar aus dem Uni-Netzwerk.
- [3] STMicroelectronics. *2N2222: NPN General Purpose Transistor*. Geneva, Switzerland, 2013. Rev. 3, March 2013.