

ELECTRON DEVICES

NOTES

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...it's negligible...

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If you want to find the source code of this pdf or more material of other topics please visit my
github account
<https://github.com/matteobaldo>

Chapter 1

Semiconductors basics

1.1 Material distinction and energy gap

Distinction between materials

In silicon-crystal electrons are subjected to periodical potential as a consequence to periodic disposition of atoms. We have bands of permitted energy level divided by gaps.

Important bands are valence band VB, that is the last band fully filled with electrons at 0 K, and conduction band CB, that is the first band totally empty of electrons. Between these 2 bands there is the so called bandgap.

We can classify all materials in 3 categories:

Metals - $E_{gap} = 0$ or small ¹ and $\rho < 10^{-2} \Omega \text{cm}$.

Semiconductors - $E_{gap} = 1 \text{eV}$ and $10^{-2} < \rho < 10^5 \Omega \text{cm}$.

Insulators - $E_{gap} > 7 \text{eV}$ and $\rho > 10^5 \Omega \text{cm}$.

Energy gap function of T

In Si $E_{gap} = 1.12 \text{eV}$ at room temperature (RT) but this value is a function of T; at high temperatures the silicon stretches and so does the periodical potential that influences the electrons. The relation of E_{gap} with temperature is

$$E_{gap}(T) = E_{gap}(0) - \frac{\alpha T^2}{\beta + T} \quad (1.1)$$

where α and β change from material to material.

We can consider a sensitivity parameter of the temperature as

$$\frac{dE_{gap}(T)}{dT} = \frac{-2\alpha T(\beta + T) + \alpha T^2}{(\beta + T)^2} \quad (1.2)$$

At RT for Si we have a change of 25meV over 100 degrees.

1.2 Silicon concentration

Conduction Band

¹BV partially empty BC completely empty or overlapped BV BC

Using the effective band approximation we want to know the density of states in CB or VB and after this the number of e or h in this bands.

Referring to the space of momentum we can say that

$$E - E_c = \frac{\hbar^2 k_x^2}{2m_x} + \frac{\hbar^2 k_y^2}{2m_y} + \frac{\hbar^2 k_z^2}{2m_z} \quad (1.3)$$

The iso-energetic surface in the space of momentum is an ellipsoid that is longer in the direction with effective mass higher. In the case 2 effective mass are equal we obtain a rotation ellipsoide just as the case of Si in witch we have $m_x = m_z = 0.19m_0 = m_t$ and $m_y = 0.92m_0 = m_l$.

Observing that energy and the ellipsoide dimentions are directly proportional we can say that all the points inside the ellipsoide have less energy than border ones.

The volume of the ellipsoide is

$$\mathcal{V} = \frac{4}{3}\pi \sqrt{\frac{2m_x(E - E_c)}{\hbar^2}} \sqrt{\frac{2m_y(E - E_c)}{\hbar^2}} \sqrt{\frac{2m_z(E - E_c)}{\hbar^2}} = \frac{4}{3}\pi \frac{\sqrt{8m_x m_y m_z}}{\hbar^3} \sqrt{(E - E_c)^3} \quad (1.4)$$

So the density of states will be

$$N = \frac{\mathcal{V}}{\left(\frac{2\pi}{L}\right)^3} \frac{1}{L^3} \quad (1.5)$$

Making thefirst derivative of the equation by dE we can obtain finally the density of states per unit energy

$$g_c(E) = \frac{4\pi}{h^3} \sqrt{2m_x m_y m_z} \sqrt{E - E_c} \cdot 2 \cdot deg \quad (1.6)$$

where the last 2 terms are a corrective coefficients for the spin and the degeneration of the material we consider (for silicon deg=6).

We can say how many states are occupied only in a very specific case of thermodynamical equilibrium². If this condition is satisfacted we can use the Fermi-Dirac statistic

$$f(E) = \frac{1}{1 + e^{(E - E_f)/kT}} \quad (1.7)$$

where E_f is the Fermi level defined as the level at which the prbability of occupation of an energy state by an electron is 1/2. $f(E)$ makes a smooth transition from 1 to 0 as the energy increases; the width of the transition is governed by kT. That can be approximated with the Maxwell-Bolzmann statistic if $E - E_f \gg kT$

$$f(E) \simeq e^{-\frac{E - E_f}{kT}} \quad (1.8)$$

This is a good approximation if we are well above E_f (at least a few kT).

Concentration of electrons in CB is (under the condition of thermodynamic equilibrium)

$$n = \int_{E_c}^{+\infty} g_c(E) f(E) dE \quad (1.9)$$

Making a change of variable as $x = (E - E_c)/kT$ and $\eta = (E_f - E_c)/kT$ we can write

$$n = \left[\frac{4 \cdot 2 \cdot deg \cdot \pi}{h^3} (kT)^{3/2} \frac{\sqrt{\pi}}{2} \right] \frac{2}{\sqrt{\pi}} \int_0^{+\infty} \frac{\sqrt{x}}{1 + e^{x - \eta}} dx = N_c \frac{2}{\sqrt{\pi}} \cdot F_{1/2}(\eta) \quad (1.10)$$

²In thermodynamic equilibrium there are no net macroscopic flows of matter or of energy, either within a system or between systems. In a system in its own state of internal thermodynamic equilibrium, no macroscopic change occurs.

where N_c is the density of states $F_{1/2}(\eta)$ is the Fermi-Dirac integral of order 1/2. Assuming $x - \eta \gg 1$ (that is the M-B approximation) we arrive at

$$n = N_c \frac{2}{\sqrt{\pi}} e^\eta \int_0^{+\infty} \sqrt{x} e^{-x} dx = N_c e^\eta = N_c e^{-\frac{E_c - E_f}{kT}} \quad (1.11)$$

Valence band

Valence band of silicon has 3 sub-bands: heavy hole band and light hole that stay at VB level and the split-off band that stays 44meV under the VB. This 3 band mass are isotopic so the iso-energetic surface in the k space are spheres; bigger the sphere bigger the effective mass. We take into account for calculations only heavy hole band:

$$E_v - E = \frac{\hbar^2 k^2}{2m_{hh}} \rightarrow \hat{k}_{hh} = \frac{\sqrt{2m_{hh}(E_v - E)}}{\hbar} \quad (1.12)$$

as done before we calculate the volume of the sphere and the number of state per unit volume

$$\mathcal{V} = 4/3 \frac{\pi}{\hbar^3} \sqrt{8m_{hh}^3} \sqrt{(E_v - E)^3} \quad (1.13)$$

$$N = \frac{\mathcal{V}}{L^3} \frac{1}{2\pi} \quad (1.14)$$

we can calculate the density of states as

$$g_V(E) = \frac{4\pi}{h^3} \sqrt{2m_{hh}^3} \sqrt{E_v - E} \cdot 2 \cdot deg \quad (1.15)$$

we proceed as for the CB obtaining the total concentration per unit volume of holes that is

$$p = p_{hh} + p_{lh} + p_{so} \quad (1.16)$$

but the concentration of holes in the split-off band is negligible due to the distance from the valence band (the transition of 1-f(E) that stays in a few kT).

$$p \simeq N_v e^{-\frac{E_f - E_v}{kT}} \quad (1.17)$$

Intrinsic and estrinsic Silicon

For intrinsic Si $p=n$ and so we can calculate E_f from this eq as

$$E_f = \frac{E_c + E_v}{2} - \frac{kT}{2} \ln(N_c/N_v) = E_i \quad (1.18)$$

E_i is the intrinsic level that stays in the middle of the gap (the correction is in the order of 0.3kT so negligible).

Putting 1.18 into p expression we obtain

$$p = n = \sqrt{N_c N_v} e^{-\frac{E_{gap}}{2kT}} = n_i \quad (1.19)$$

n_i is the intrinsic carrier concentration that has a strong dependance with T as it is involved in $N_c, N_v \propto (kT)^{3/2}$ and in E_{gap} .

From 1.11 by adding and subtracting E_i and dividing the exponential in 2 parts we can write

$$n = n_i e^{(E_f - E_i)/kT} \quad p = n_i e^{(E_i - E_f)/kT} \quad (1.20)$$

this are 2 expressions valid in general not only for intrinsic semiconductors.
We can introduce the law of mass action as

$$pn = n_i^2 \quad (1.21)$$

For estrinsic semiconductors ,in the band diagram ,there is another band near to CB (E_d) (or near to VB E_a depending on the type of dope).

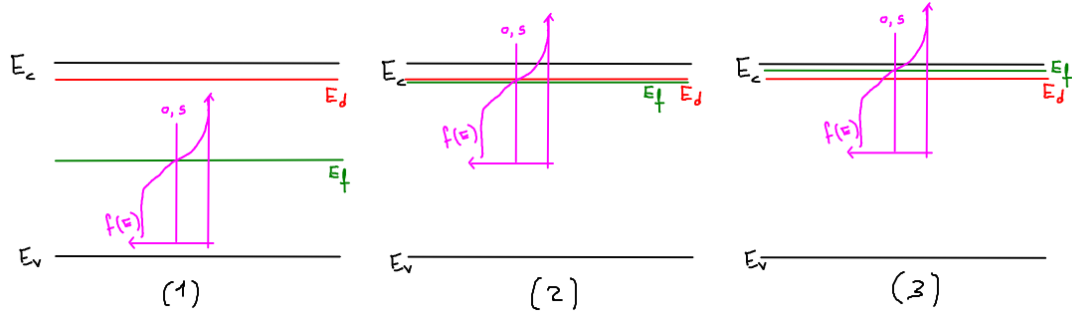
We want to estimate the position of E_f in n-doped Si. We can write that $n = p + N_d^+$ where N_d^+ are the ionized donor concentration so

$$n = p + N_d(1 - \frac{1}{1 + \frac{1}{2}e^{(E_d - E_f)/kT}}) = p + \frac{N_d}{1 + 2e^{-(E_d - E_f)/kT}} \quad (1.22)$$

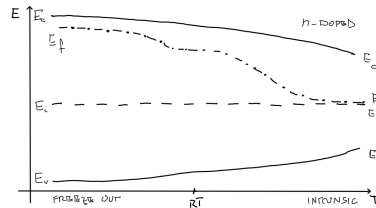
the factor $1/2$ it's a spin correction coefficient. At RT $E_d - E_f \gg kT$ and p concentration is negligible in comparison with N_d so $n \simeq N_d$ and from the law of mass action $p = n_i^2/N_d$. From this we can compute E_f as

$$E_c - E_f = kT \ln(N_c/N_d) \quad (1.23)$$

Moving E_f upwards some hypothesis falls (we supposed E_f to be under E_d) : when E_f reaches E_d the complete ionization theory is not true anymore (2) ,since in that case $n = p + N_d/3$, and from there further the M-B approximation is no longer valid (3) ,not all states over conduction band are empty.



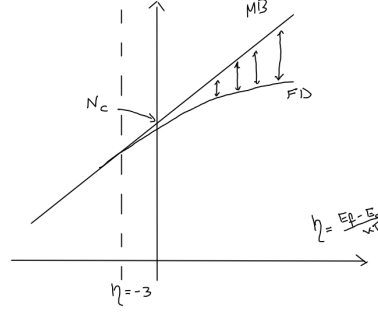
Fermi level dependence on temperature in doped semiconductors



With high T E_g decreases and E_f will move distant to E_c following $E_f = E_c - kT \ln(N_c/N_d)$ until the hypothesis of negligible holes concentration decays and so at very high temperatures E_f will tend asymptotically to E_i .

At very low temperature E_f will increase until we reach the 0K where there is no conduction so E_f has to stay a little bit higher than E_d .

Low-temperature approssimation



In the case of a material that has its Fermi level higher than the conduction band level we cannot use the M-B approximation. The approximation we can do is a low-temperature one that transforms the Fermi Dirac distribution into a step so

$$n = \int_{E_c}^{E_f} \frac{48\pi}{h^3} \sqrt{2m_t^2 m_l} \sqrt{E - E_c} \quad (1.24)$$

that multiplying and dividing the result by $(kT)^{3/2} \sqrt{\pi}/2$ we obtain

$$n = N_c 2/3 \frac{2}{\sqrt{\pi}} \left(\frac{E_f - E_c}{kT} \right)^{3/2} = N_c 2/3 \frac{2}{\sqrt{\pi}} \eta^{3/2} \quad (1.25)$$

In the graph above we can notice the difference between F-D and M-B distribution over η .

1.3 Current transport

There are 4 main mechanisms that contribute to current transport; drift, diffusion, thermoionic transport and tunneling effects. Among this 4 the first 2 are the most important and frequent.

Drift current is caused by the application of a electric field F ; electrons are not only influenced by F but also from scattering events so we can define a drift velocity (that is an average velocity) as

$$v_d = \mu_n F \quad (1.26)$$

So drift velocity is proportional to F with a constant μ_n called mobility that depends on doping concentration, temperature and dimensionality of the system taking in account all scattering events. It's important to note that in a bulk of doped Si if we are near the surface the mobility is much lower than the inside (dimensionality dependance).

Mobility has a drop for Si around doping concentration of $\simeq 10^6 \text{ cm}^{-3}$ beacuse at that level scattering with impurities becomes dominant compared with thermal scattering.

Increasing too much F we encounter the phenomena of velocity saturation ($v_{sat} \simeq 10^7 \text{ cm/s}$) caused by scattering with high energetic optical phonons.

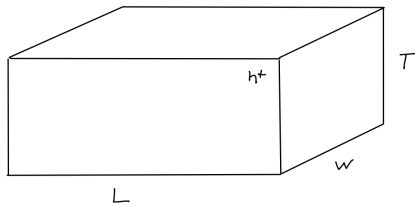
The density current caused by drift process is

$$J = (qn\mu_n + qp\mu_p)F = \sigma F = F/\rho \quad (1.27)$$

where σ is the conductivity of the material and ρ is the resistivity.

When we

calculate the resistivity of a block of doped silicon like in figure we define $\rho_{sh} = \rho/T$ as the sheet resistivity



$$R = \rho \frac{W}{LT} = \rho_{sh} \frac{W}{L} \quad (1.28)$$

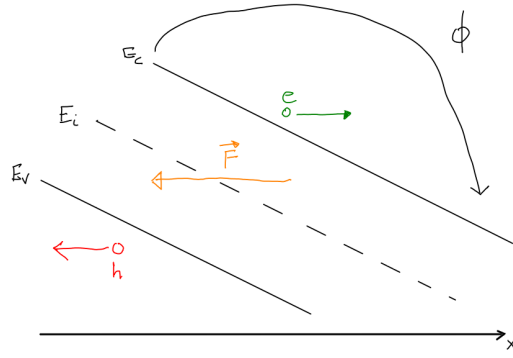
Diffusion current is driven by
a gradient of concentration so the density of current is

$$J_n = qD_n \frac{dn}{dx} \quad J_p = qD_p \frac{dp}{dx} \quad (1.29)$$

where D_n, D_p are the diffusion coefficients defined by Einstein's relations as

$$D_n = \mu_n \frac{kT}{q} \quad D_p = \mu_p \frac{kT}{q} \quad (1.30)$$

1.4 Bands "geography"



We can obtain external potential ϕ as $\phi = \frac{-E_i(x)}{q}$.

The external potential increases in the direction the bands bend downwards. The electric field is in the opposite direction of the growth of potential $\vec{F} = -\frac{d\phi}{dx}$.

Electrons move by drift in the opposite direction of F and holes in the same direction of F .

1.5 Poisson equation

Poisson equation is important to study the electrostatic of a system.

We can derive it from Maxwell's first law

$$\vec{F} = -\vec{\nabla}\phi \rightarrow F = -\frac{d\phi}{dx} \quad (1.31)$$

and Gauss equation

$$\vec{\nabla} \cdot \vec{F} = \rho / \epsilon_{Si} \quad (1.32)$$

from which we obtain considering that all charges we have in a semiconductor are holes, electrons and ionized donors

$$\frac{d^2\phi}{dx^2} = -\rho / \epsilon_{Si} = -\frac{q}{\epsilon_{Si}}(p - n + N_d^+ - N_a^-) \quad (1.33)$$

In order to study the electrostatic of a system we have also to know the continuity equations of the electric field that are

$$F_{t1} = F_{t2} \iff \epsilon_1 F_{n1} - \epsilon_2 F_{n2} = Q'_{int} \quad (1.34)$$

1.6 Debye length

Band bending is the phenomena caused by applying an electric field on a material at thermodynamic equilibrium. This band bending causes different concentrations of e and h over the space so we can re-write the electron and holes concentrations taking in account the change of $\phi(x)$ over the space as

$$n = n_i e^{q \frac{\phi(x) - \phi_f}{kT}} \quad p = n_i e^{q \frac{\phi_f - \phi(x)}{kT}} \quad (1.35)$$

This band bending is also caused by the change of doping concentration over the space. With a smooth change of N_d in a material we can assume that $n = N_d$.

Let's assume a step-like function in doping concentration in this case we cannot consider $n = N_d$ over the space because this assumption will lead us to an infinite electric field.

Using Poisson equation and neglecting holes and ionized acceptors we can say that $N_d(x) = \hat{N}_d + \delta N_d(x)$ corresponding to $\phi(x) = \hat{\phi} + \delta\phi(x)$ and assuming $\delta N_d \ll N_d$ we can write

$$\frac{d^2\phi}{dx^2} = -\rho/\epsilon_{Si} = -\frac{q}{\epsilon_{Si}}(\hat{N}_d + \delta N_d(x) - n_i e^{q \frac{\hat{\phi} + \delta\phi(x) - \phi_f}{kT}}) = -\frac{q}{\epsilon_{Si}}(\hat{N}_d + \delta N_d(x) - \hat{N}_d e^{q \frac{\delta\phi(x)}{kT}}) \quad (1.36)$$

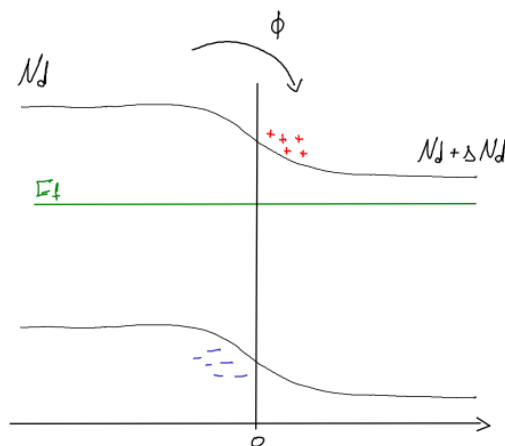
we can write the first order expansion of the exponential term because the exponent is small ($e^{q \frac{\delta\phi(x)}{kT}} \simeq 1 + q \frac{\delta\phi(x)}{kT}$) obtaining the following differential equation

$$\frac{d^2\phi}{dx^2} = \frac{q^2 \hat{N}_d}{\epsilon_{Si} kT} \phi(x) - \frac{q}{\epsilon_{Si}} \delta N_d(x) \quad (1.37)$$

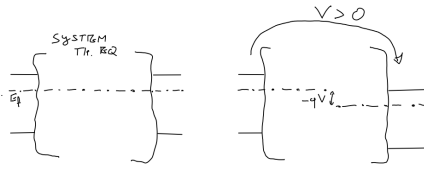
the solution of this equation give us an exponential increase of the potential (and so a decrease of the bands) with a length called Debye length

$$L_D = \sqrt{\frac{\epsilon_{Si} kT}{q^2 N_d}} \quad (1.38)$$

this will cause a net charge (both negative and positive near the discontinuity).



1.7 Quasi-Fermi levels



For having a net current transport (we're leaving the thermodynamic equilibrium hypothesis) we have to perturb our system by for example applying at the contact ³ a $V \neq 0$. As the figure shows we can't introduce a E_f level and so we cannot use the FD distribution. If the perturbation is weak we can recover all expressions of th.eq by introducing different

Fermi levels both for e and h called quasi Fermi levels

$$n = n_i e^{\frac{E_{fn} - E_i}{kT}} \quad p = n_i e^{\frac{E_i - E_{fp}}{kT}} \quad (1.39)$$

so we can write the law of mass action generalized as

$$pn = n_i^2 e^{\frac{E_{fn} - E_{fp}}{kT}} \quad (1.40)$$

Now let's try to analyse the total current density of electrons. The formula has a strong dependance from the electrostatic potential (from F and n) so

$$J_n = qn\mu_n F + qD_n \frac{dn}{dx} = -qn\mu_n \frac{d\phi}{dx} + qD_n \frac{d}{dx} \left(n_i e^{q\frac{\phi - \phi_f}{kT}} \right) = -qn\mu_n \frac{d\phi_f}{dx} \quad (1.41)$$

But since the Fermi potential is constant the result is 0 and it's obvious because we assume th.eq. with formula (1.20). If we substitute the (1.39) in n we obtain

$$J_n = -qn\mu_n \frac{d\phi_{fn}}{dx} \quad (1.42)$$

$$J_n = n\mu_n \frac{dE_{fn}}{dx} \quad (1.43)$$

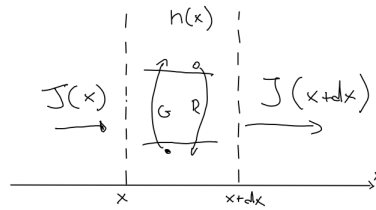
that isn't 0 because ϕ_{fn} can change.

Electrons move from the region of high quasi Fermi level to region of low quasi Fermi level, holes the opposite.

$$J_p = -qp\mu_p \frac{d\phi_{fp}}{dx} \quad (1.44)$$

$$J_p = p\mu_p \frac{dE_{fp}}{dx} \quad (1.45)$$

1.8 Equation of for e and h



³region of dispositive from which we can externally apply a F , a good contact stays at th. eq.

Let's consider the figure above if we make a ballace of charges between x and $x+dx$ we have

$$\frac{\partial n}{\partial t} dx = -J_n(x)/q + J_n(x+dx)/q + (G-R)dx \quad (1.46)$$

where G and R are generation and ricombination processes per unit time per unit volume. If we expand at the first order $J(x+dx) \simeq J_n(x) + \frac{\partial J_n}{\partial x} dx$ and simplify the expression we have

$$\frac{\partial n}{\partial t} = \frac{1}{q} \frac{\partial J_n}{\partial x} + G - R \quad \frac{\partial p}{\partial t} = -\frac{1}{q} \frac{\partial J_p}{\partial x} + G - R \quad (1.47)$$

that are the continuity equation for electrons and hole current.

In a stationary system nothing change with time so subtracting the 2 equation we have

$$\frac{\partial(J_n + J_p)}{\partial x} = 0 \quad (1.48)$$

so the sum of the 2 contributions of current from e and h stay costant. If we neglect G and R the 2 contrbutes are costant separatly.

G and R process restabilize equilibrium of a system if we perturb the minority carrier concentration. If we disturb majority carrier the system returns in equilibrium with a very short time costant. Let's analyse the 2 case.

Majority carrier perturbation

Assume a n-doped material and let us add Δn concentration of electrons. Using poisson equation we have

$$\frac{\partial \phi^2}{\partial x^2} = -\frac{q}{\varepsilon} (-n - \Delta n + N_d) = \frac{q\Delta n}{\varepsilon} = -\frac{dF}{dx} \quad (1.49)$$

from this result we obtain a field that has a linear dependence over the space that tends to move away the excess of charge with a drift current (no diffusion the concentration is costant) so using 1.44

$$\frac{\partial J_n}{\partial x} = qn\mu_n \frac{\partial F}{\partial x} \quad (1.50)$$

$$\frac{\partial n}{\partial t} = \frac{1}{q} \frac{\partial J_n}{\partial x} = -\frac{1}{q} qn\mu_n \frac{q\Delta n}{\varepsilon} = -\frac{\Delta n}{\varepsilon\rho} \quad (1.51)$$

solving this differential equation we have a solution that has an exponential dependence with $\varepsilon\rho$ that is called the diaelectric relaxation time of the material; it's the time costant that the system use to return to its equilibrium ($\simeq ps$)

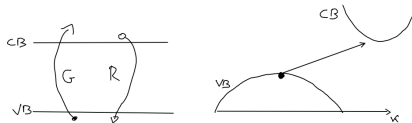
Minority carrier perturbation

The phenomena described for majority carrier concentration isn't valid for minority carrier.

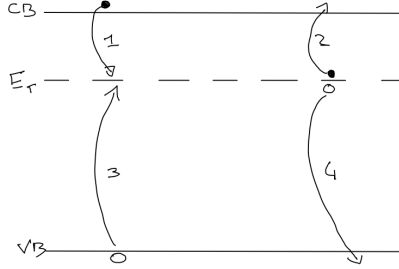
Considering a n-doped material like before the ρ in equation 1.48 is very high (we are considering holes now) the J_p curret isn't able to move a lot of holes so the real result of the field is that attracts a concentration Δn over Δp creating a quasi-neutral region where G and R slowly decrease the 2 extra concentration.

In the processes of G and R in Si electrons cannot move through the bandgap from CB to VB they need another particle to respect the conservation of momentum.

We need a difect of the cristal that creates another "band" in the bandgap this process called difect assisted and is described by Shockley-Reed-Hall theory.



releases an hole from VB.



The difect can only be empty or filled with one electron so there can be only 4 process: 1) Difect empty captures e from CB 2) Difect filled realeses an e to CB 3) Difect filled captures hole from VB 4) Difect empty

For R we need 1 and 3 for G 2 and 4.

The rate of 1 can be described as

$$r_1 = N_T(1 - f(E_T))n(v_{th}\delta_n) \quad (1.52)$$

where: N_T is the total difect concentration
,f probability of the difect to be filled and the last term is a costant where δ_n is the capture crossection.
The rate of process 2 can be described as

$$r_2 = N_T f(E_T) e_n \quad (1.53)$$

where e_n is a proportionality costant emission rate for e. Under th.eq. $r_1 = r_2$ and we can use the FD distribution for f. Under this condition we can calculate e_n (and using the same consideration also for process 3 and 4 and so obtaining e_p)

$$e_n = n_i v_{th} \delta_n e^{\frac{E_T - E_i}{kT}} \quad e_p = n_i v_{th} \delta_p e^{\frac{E_i - E_T}{kT}} \quad (1.54)$$

There is an exponential dependance if the difect is colser to the conduction band the process of release is higher; vice-versa the process of capture doesn't have this dependance beacuse the e has only to realese energy.

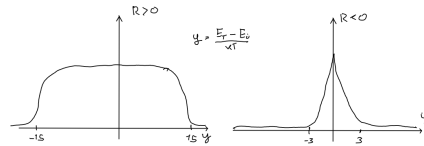
Under stationary condition $R = r_1 - r_2 = r_3 - r_4$ from this we obtain $f(E_T)$ and we get the final result

$$R = \frac{pn - n_i^2}{\tau_0 [p + n + 2n_i \cosh(\frac{E_T - E_i}{kT})]} \quad (1.55)$$

where $\tau_0 = 1/(v_{th}N_T\delta)$ and we've assumed $\delta_n = \delta_p = \delta$.

Re-writing the numerator using $n = n_i e^{(E_{fn} - E_i)/kT}$ $p = n_i e^{(E_{fp} - E_i)/kT}$ we can obtain that if $E_{fn} > E_{fp} \rightarrow R > 0$ and if $E_{fn} < E_{fp} \rightarrow R < 0$.

Looking at the graph of R in the 2 case major of less than zero we can make a few considerations



$R > 0$ relevant part in the denominator is $p+n$ but over 15 the Cosh becomes dominant so we get the drop.

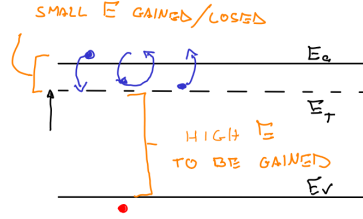
$R < 0$ Cosh is always dominant so we have from the beginning a rapid drop beacuse $p+n$ are few and the system is generating couples.

Phisical explanation can be given from a particular case.

We want to study only recombination so $R = \nu_1 = \nu_3 = (1 - f(E_T))n = f(E_T)p$ so we can caluclate $f(E_T) = n/(n + p)$ and so $R = N_T v_{th} \delta \frac{pn}{p+n} = \frac{pn}{\tau_0(n+p)}$ that is a semplification of the

general formula we have a flat recombination rate because 1,3 processes have only to lose energy the drop is caused by the growing relevance of 2 or 4 moving E_T near to CB of VB. The best position for the defect is on the middle of the gap. Maximum G is when $p=n=0$ so $G = -n_i/2\tau_0$.

The rapid drop can also be explained physically taking into account that more the trap energy level moves from the middle of the gap (to conduction band for example) more becomes easy for an electron to have enough energy to jump in CB and hard for a hole to arrive in VB. Also an electron from CB can occupy the empty energy state easily since it has to lose a small amount of energy. We arrive in a condition when electrons recirculate and holes "cannot" participate in the process.



1.9 Quasi-neutral condition

Under quasi-neutral condition $\Delta n + n_0 = n$ and $\Delta p + p_0 = p$ assuming low injection level ($\Delta n \ll p_0 + n_0$) we can neglect in the eq of R all the terms with " Δ " so we obtain

$$R = \frac{(p_0 + n_0)\Delta n}{\tau [p_0 + n_0 + 2n_i \cosh(\frac{E_T - E_i}{kT})]} = \frac{\Delta n}{\tau_n} \quad (1.56)$$

if we suppose $E_T - E_i = 0$ $\tau_n \simeq \tau_0 = 1/(N_T v_{th} \delta)$
So the continuity equation for electrons becomes ⁴

$$-\frac{d\Delta n}{dt} = R \rightarrow \Delta n \propto e^{-t/\tau_n} \quad (1.57)$$

where τ_n is dependent on the quality of the material

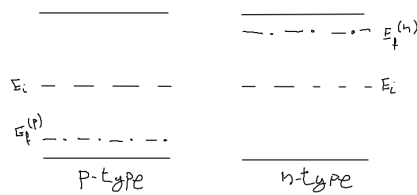
⁴Minus sign in the expression comes from G-R we are considering -R

Chapter 2

Diodes

Diodes or pn junction are basically 2 zones of opposite doping polarity attached together. To study pn junctions we have to make some simplifying assumptions : we consider 1D materials with constant doping concentration and a step-like change of doping from p to n.

2.1 Built-in potential



Let's consider the 2 regions isolated from each other and under th.eq. We don't have a single Fermi level so depending on the zone we have

$$E_i - E_f^{(p)} = kT \ln\left(\frac{N_a}{n_i}\right) \quad E_f^{(n)} - E_i = kT \ln\left(\frac{N_d}{n_i}\right) \quad (2.1)$$

where $E_f^{(n/p)}$ is the Fermi level in that zone.

When we put the 2 materials together there will be first a diffusion current and then also a drift current

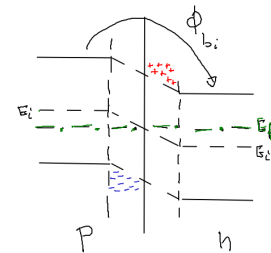
due to the band bending and the exposed charge; we will reach th.eq when the total current will be 0.

Under th.eq we

will have a constant Fermi level all over the space and a band bending at the interface. Far from the interface we will reach zones where the bands are like the isolated case. The drop of electrostatic potential in the junction under th.eq is called built in potential or ϕ_{bi} and is

$$q\phi_{bi} = (E_f^{(n)} - E_f^{(p)})|_{n.e} = kT \ln\left(\frac{N_a N_d}{n_i^2}\right) \quad (2.2)$$

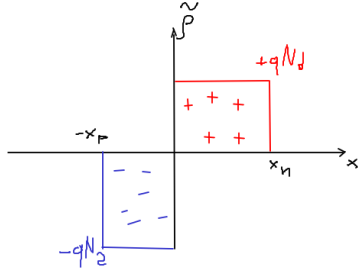
that is close to the E_g of the material.



2.2 Depletion approximation

Because the distance $E_f - E_c$ increases near the junction we have an exponential decrease of n so in the transition region we can say that $n \ll N_d$ and so $p \ll N_a$. From this we can say that the transition region is depleted of free carriers because their concentration is negligible so this region is called depletion region.

2.3 Electrostatics of a pn junction



junction as

We have to solve

Poisson equation in the depletion region so using depletion approximation and considering complete ionization

$$\frac{d^2\phi}{dx^2} = -\frac{q}{\epsilon}(N_d - N_a) \quad (2.3)$$

and considering

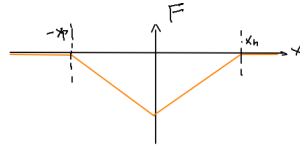
the concentration of fixed charges like the graph

we can split the Poisson eq in 2 parts for $-x_p < x < 0$ we

have $\frac{d^2\phi}{dx^2} = \frac{q}{\epsilon}N_a$ and for $0 < x < x_n$ we have $\frac{d^2\phi}{dx^2} = -\frac{q}{\epsilon}N_d$.

If we integrate both sides of this equation and remembering that $F(x_n) = 0$ we can deduce the electric field in the

$$\int_x^{x_n} d\left(\frac{d\phi}{dx}\right) = \int_x^{x_n} -\frac{q}{\epsilon}N_d dx \quad (2.4)$$



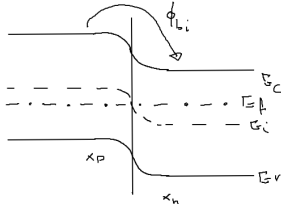
$$F(-x_p < x < 0) = -\frac{qN_a}{\epsilon}(x_p + x) \quad F(0 < x < x_n) = -\frac{qN_d}{\epsilon}(x_n - x) \quad (2.5)$$

for continuity

equations of the electric field the F must be continuous in 0 so from this condition we get that $N_a x_p = N_d x_n$ that means that the total charge in the depletion area is 0 (from Gauss law also).

Integrating

again both parts of the equation of the field we finally obtain the potential over the space that has a parabolic dependence



$$\phi(-x_p < x < 0) = \phi(-x_p) + \frac{qN_a}{2\epsilon}(x+x_p)^2 \quad \phi(0 < x < x_n) = \phi(x_n) - \frac{qN_d}{2\epsilon}(x_n-x)^2 \quad (2.6)$$

To know x_n and x_p we have to set some boundary condition: ϕ must be continuous in 0, and $N_a x_p = N_d x_n$ from this 2 conditions we get

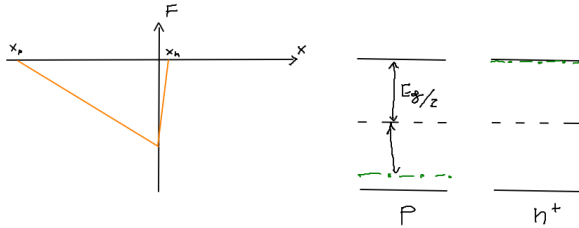
$$x_n = \sqrt{\frac{2\epsilon}{q} \phi_{bi} \left(\frac{1}{N_a} + \frac{1}{N_d} \right)} \times \frac{N_a}{N_a + N_d} \quad x_p = \sqrt{\frac{2\epsilon}{q} \phi_{bi} \left(\frac{1}{N_a} + \frac{1}{N_d} \right)} \times \frac{N_d}{N_a + N_d} \quad W = \sqrt{\frac{2\epsilon}{q} \phi_{bi} \left(\frac{1}{N_a} + \frac{1}{N_d} \right)} \quad (2.7)$$

Order of magnitude for the depletion layer given N the doping concentration of the less doped

zone:

$N_{d/a}$	W_d
10^{16}	300nm
10^{17}	100nm
10^{18}	10nm

2.4 Unilateral Junction



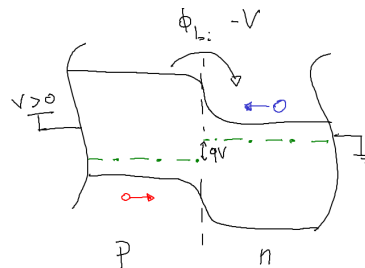
Let's consider a junction n^+p so the depletion area is almost all in the less doped material and so the electric field. We can make some approximation that the depletion area is almost in the p zone and that the Fermi level of the n^+ zone is almost at E_c so this lead us to

$$W \simeq x_p \quad q\phi_{bi} \simeq E_g/2 + kT \ln\left(\frac{N_a}{n_i}\right) \quad (2.8)$$

2.5 Bias

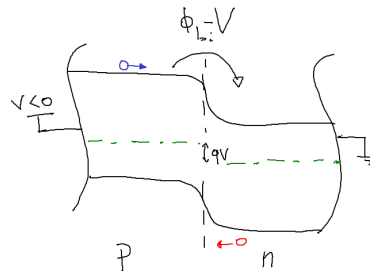
To better understand this paragraph draw the below graphs with also the electric field due to the external applied voltage.

Forward Bias



Applying a external voltage like in figure we are reducing the total voltage drop over the junction. There will be a net flow of electrons from left to right that is a current by diffusion that will be large because we have a lot of charges.

Reverse Bias



In this case $V < 0$ electrons and holes move for drift the total voltage drop will be greater than the built in. The flow of current is given by minority carrier so small I.

2.6 The V-I characteristic of pn

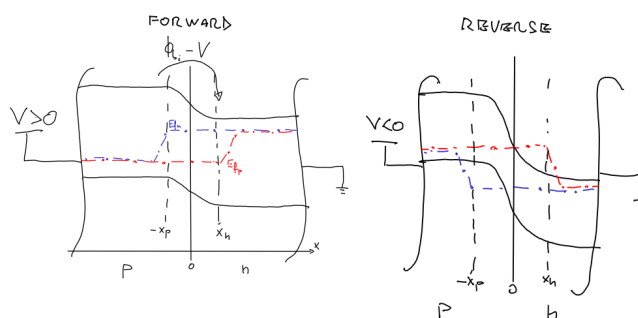
We want to investigate on forward bias electrostatic but we have to make some other simplifying assumption: the contacts of our junction are at th.eq. and looking to the n region moving closer to the contact (from the interface) we will enter in a region where electrons are majority carrier. Beacuse we are injecting holes in that region we will have $p = p_{n0} + \Delta p$ so a region of quasi-equilibrium.

If we assume stationarity and that G and R process are negligible and so the

$$J_n = n\mu_n \frac{dE_{fn}}{dx} = \text{const.}$$

Beacuse n isn't costant all over the space (space of all the diod first n minority than majority) $\frac{dE_{fn}}{dx}$ will change over the space.

Being the grandient of n very small near the contacts E_{fn} will be almost flat as conduction and valence bands in that region. The final graph is this



we have 2 region of quasi-equilibrium and a transition region that is depleted from free charges.

We can divide the a zone in 3 regions and analyse the the two factors n and $\frac{dE_{fn}}{dx}$:

Near the contact: small gradient of n so also small change of $\frac{dE_{fn}}{dx}$ that we can assume quasi-constant.

Depleted region: free carriers are negligible and so "constant" all over that zone so also here quasi-constant $\frac{dE_{fn}}{dx}$.

Opposite transition region: here the values of n rapidly drops until it reaches the equilibrium value so there will be a noticeable $\frac{dE_{fn}}{dx}$.

This is the same result of electrostatic without bias so the depletion region will be

$$W = \sqrt{\frac{2\varepsilon}{q}(\phi_{bi} - V)\left(\frac{1}{N_a} + \frac{1}{N_d}\right)} \quad (2.9)$$

E_{fn} remains almost¹ costant until $-x_p$ but n changes beacuse E_c moves upwards.

For reverse bias we have to follow the same path of forward bias arriving at the graph above. Bands are flat near the contact beacuse we suppose (1) quasi-neutral region under (2) low level of injection with (3) costant doping and (4) negligible gradient of quasi-Fermi levels; if one of this supposition falls the bands will no more be flat.

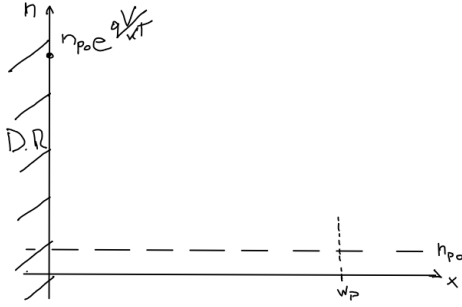
Now we want to know the quasi-Fermi level in the minority region. We know that at $x = x_n$ $n \simeq N_d$ and for the law of mass action generalized $p = \frac{n_i^2}{N_d} e^{\frac{E_{fn} - E_{fp}}{kT}} \simeq p_{n0} e^{\frac{qV}{kT}}$ and at $x = -x_p$ with the same passages we obtain $n \simeq n_{p0} e^{\frac{qV}{kT}}$. Now we can solve the continuity equation only in the quasi-neutral region.

¹if E_{fn} is constant its gradient is zero and there is no current flowing according to previous expressions

Beacuse the bands are flat we have only diffusion so $J_n = qD_n \frac{dn}{dx}$ and $G - R = \frac{-\Delta n}{\tau_n}$ from this two in the coninuity equations under stationary condition we get

$$\frac{d^2 \Delta n}{dx^2} - \frac{\Delta n}{L_n^2} = 0 \quad (2.10)$$

where $L_n = \sqrt{D_n \tau_n}$ = diffusion length of electrons in the quasi neutral p-region. Introducing the system of coordinate like in figure (where W_p is the end of the quasi-neutral p region and so of the device) we can solve this differential equation.



Solving that

as a polynomial we get $\lambda^2 - \frac{1}{L_n^2} = 0 \leftarrow \lambda = \pm \frac{1}{L_n}$

so we get two exponential terms that are $\Delta n(x) = Ae^{\frac{x}{L_n}} + Be^{-\frac{x}{L_n}}$ using the boundary condition $\Delta n(0) = n_{p0}(e^{\frac{qV}{kT}} - 1)$ and $\Delta n(W_p) = 0$ we arrive at

$$\Delta n(x) = n_{p0}(e^{\frac{qV}{kT}} - 1) \frac{\sinh(\frac{W_p - x}{L_n})}{\sinh(\frac{W_p}{L_n})} \quad (2.11)$$

Having only diffusion processes we

can know the current but we are intrested only² in $J_n(0)$ at the edge of the quasi-neutral region so

$$J_n(0) = (qD_n \frac{d\Delta n}{dx})|_{x=0} = -\frac{qD_n n_{p0}}{L_n \tanh(W_p/L_n)} (e^{\frac{qV}{kT}} - 1) \quad (2.12)$$

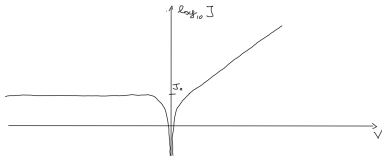
so in general the total current in the pn junction is

$$J = [\frac{qD_n n_{p0}}{L_n \tanh(W_p/L_n)} + \frac{qD_p p_{n0}}{L_p \tanh(W_n/L_p)}] (e^{\frac{qV}{kT}} - 1) = J_0 (e^{\frac{qV}{kT}} - 1) \quad (2.13)$$

If $V \gg kT/q$ we can neglect

1 and plot a log-log scale of this characteristic that is

$$\log(J) = \log(J_0) + \frac{qV}{kT \ln(10)} \quad (2.14)$$

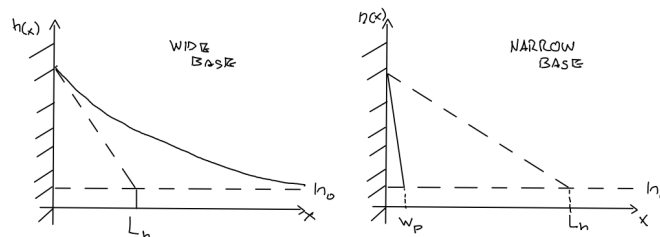


One important parameter of the characteristic is the slope in foward bias that is $kT/q \ln(10) = 60mV/dec @RT$.

The dominant contribute to the current is from the zone less doped like in the electrostatic. If we have a $n^+ - p$ junction the dominant flow is J_n ; electron flowing through the p-region injected to n-region. Current density dominated by the less doped zone minority carriers.

² The sum of electron and holes current will be constant since we are in a stationary condition so we keep interest only in one section of the device. We don't want to know the currents graphs in function of space in a rigorous way

2.7 Wide and narrow base diode

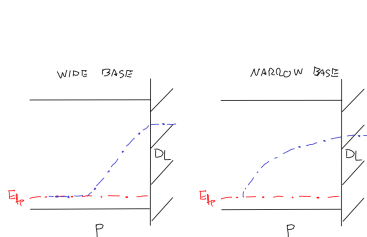


If we have a wide-base diode if $W_p \gg L_n$ so we can approximate as follow the expression of charge and of current density

$$\Delta n(x) = n_{p0}(e^{\frac{qV}{kT}} - 1)e^{\frac{-x}{L_n}} \quad J_n = \frac{qD_n n_{p0}(e^{\frac{qV}{kT}} - 1)}{L_n} \quad (2.15)$$

If we have a narrow-base diode if $W_p \ll L_n$ so we can approximate as follow the expression of charge and of current density

$$\Delta n(x) = n_{p0}(e^{\frac{qV}{kT}} - 1)\frac{W_p - x}{W_p} \quad J_n = \frac{qD_n n_{p0}(e^{\frac{qV}{kT}} - 1)}{W_p} \quad (2.16)$$



In a

wide base diode $n(x)$ decrease exponentially in the p region therefore E_{fn} will decrease linearly with a slope of kT/L_n and after the intersection with E_{fn} it will be constant.

For a narrow base the decrease of E_{fn} will be logarithmic because $n(x)$ decreases linearly.

In the quasi neutral p (n) region we have less electrons (holes) than in all other zone so the highest resistivity. The limit for conduction is given by the quasi-neutral region

where we have less concentration of minority carriers; this is why the pn junction is called a minority carriers device, the limit for current transport is given by minority carriers.

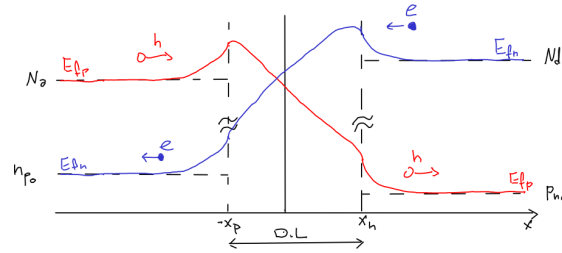
Consider a narrow base diode in reverse bias. Increasing the negative voltage applied we increase the depletion layer reducing the width of the quasi neutral region. The reverse current will increase due to the increase of the slope of carriers.

Looking at the two expressions of the current in wide and narrow base case we can notice that the J_0 stay constant changing the length of the device if we consider a wide base diode but if we consider a narrow base one J_0 will increase hyperbolically (as $1/x$) reducing W . This is due to the fact that the current is purely diffusive and reducing the length means to increase the gradient of carriers and so the current.

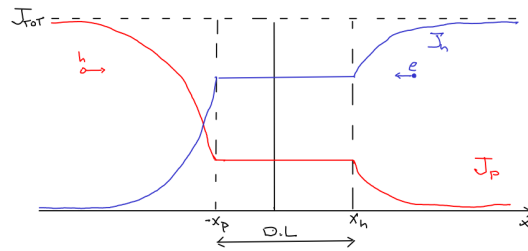
2.7.1 Current profile

Wide base forward bias

The exponential behaviour of the minority will be followed by a consequent increase of majority charges in order to maintain the region quasi-neutral. In the depletion layer a connection between the 2 region. Minority carriers moves for diffusion but majority carrier moves for drift because there is a small gradient of E_{fn} that let electrons move from right to left.

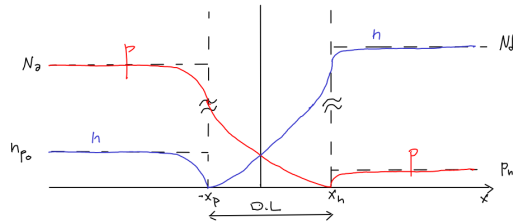


To know J_n in n region we have to remember that under stationary condition (so in quasi neutral region) $J_n + J_p = \text{const}$. Also we remember that under stationary conditions and neglecting G-R both current contributions are constant. From this considerations we can draw the graph of J_n, J_p over the space.

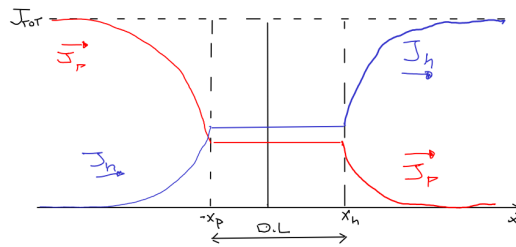


Wide base reverse bias

Same path of before : minority carrier in quasi neutral regions decrease before the depletion layer so this phenomena will be copied by the majority carrier in order to mantain quasi-neutrality.



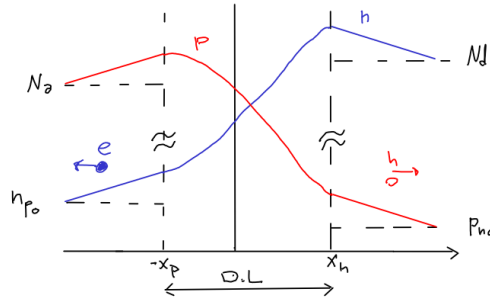
Knowing $J_n + J_p = \text{const}$ in stationary conditions and that if we neglect also G-R process we have both currents constat we obtain the following graph.



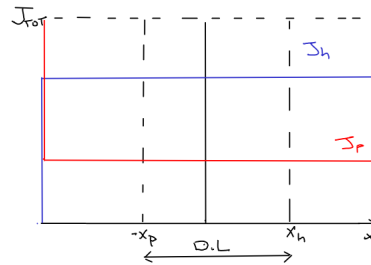
The flow of holes becomes zero at n contact but than in grows for generation processes. We have the same behaviour of the current both in reverse and in forward bias but J_{tot} changes of orders of magnitude. As before minority carriers move by diffusion, majority by drift and in the depletion layer we have movement by drift.

Narrow base forward bias

Linear increase of minority carriers so also majority in order to maintain the region quasi-neutral.

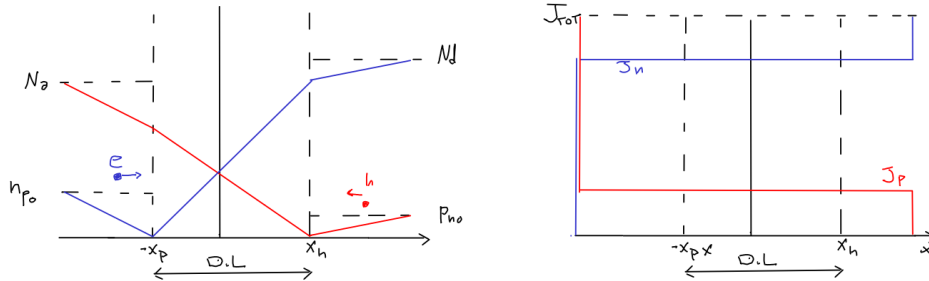


The derivate of a linear dependence is constat so J_n and J_p remain constat. There is no space to G-R process beacuse the device is much shorter than L_n so all generation and ricombination process are at the contacts.



Narrow base reverse bias

With the same path of before we arrive at



If we take into account a pn-j with dopings $N_a = 10^{16}$, $N_d = 10^{17}$ we get a diffusion lenght $L_n \simeq 310\mu m$, $L_p \simeq 110\mu m$ so it's unlikely to have a wide base diode in our integrated circuits.

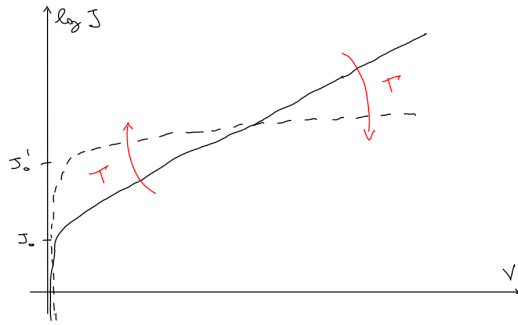
G-R effects in modern integrated devices are secondary effects that takes place only at low current.

Orders of magnitude for J_0 with $W = 1\mu m$ in case of a wide base diod is $1 pA/cm^2$ for narrow base $1 nA/cm^2$

All graphs are referred to a $p - n^+$ junction we can say that based on the concentration of carriers and also from the currents densities since the dominant contribution is always the one coming from electrons that are the minority carriers of the less doped zone.

2.8 T change

Let's consider a pn junction in forward bias $J = J_0(e^{\frac{qV}{kT}} - 1) \simeq J_0 e^{\frac{qV}{kT}}$. If we increase the T the slope of the straight part will increase for the exponential term (be careful to units in the graph the line becomes flatter) but also $J_0 = \frac{qD_n n_i^2}{N_a L_n}$ will increase for his strong dependance with temperature caused by $n_i^2 \propto T^3 e^{-\alpha/T}$.



So with the increase of T we can have both an increase or a decrease of voltage corresponding a fixed J. We have to find the typical regime of our device so from $J = J_0 e^{\frac{qV}{kT}}$ we extract the voltage as $V = \frac{kT}{q} \ln(J/J_0)$ with J a fixed current. Now we can derive obtaining

$$\frac{dV}{dT} = \frac{k}{q} \ln(J/J_0) + \frac{kT}{q} J_0/J \frac{-J \frac{dJ_0}{dT}}{J_0^2} = V/T - \frac{kT}{q} \frac{dJ_0}{dT} \frac{1}{J_0} \quad (2.17)$$

for simplicity we can highlight J_0 dependences on temperature writing $J_0 = aT^\gamma e^{-E_g/2kT}$ so

we obtain that $\frac{dJ_0}{dT} = J_0 \gamma/T + J_0 [-\frac{dE_g}{dT} \frac{1}{kT}] + J_0 \frac{E_g}{kT^2}$ so coming back at voltage we obtain

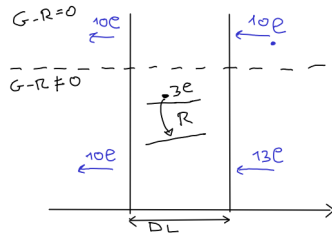
$$\frac{dV}{dT} = (V - \frac{E_g}{q}) \frac{1}{T} - \frac{k\gamma}{q} + \frac{1}{q} \frac{dE_g}{dT} \quad (2.18)$$

Since our typical $V \simeq 0.6/0.7$ there are all negative terms so we are in the first zone where we find a decrease of voltage w.r.t an increase of the temperature (at RT $dV/dT \simeq -1.9 \text{ mV/K}$)

2.9 Second order effects on current

There are some phenomena that we have to consider in order to make more realistic the J-V graph of a pn junction.

2.9.1 Low current regime



We have always neglected the G-R in the depletion layer but now we have to make some considerations.

Under reverse

bias $E_{fn} < E_{fp}$ so there will be some generation processes, knowing the quasi-Fermi level and using the law of mass action generalized we can write the SRH R coefficient as

$$R = \frac{n_i^2 (e^{qV/kT} - 1)}{\tau_0 (p + n + 2n_i Ch((E_t - E_i)/(kT)))} \quad (2.19)$$

so the sign of the voltage applied V change the sign of R.

Referring to forward bias the impact of R is that from majority region there will be more electron moving to the depletion region because of minority constrain of the pn junction. So we expect a larger current under forward bias where

$R \simeq \frac{n_i^2(e^{\frac{qV}{kT}} - 1)}{\tau_0[p+n]}$ to get the worst case we take $p=n$ so R will be maximum and we get

$$R = \frac{n_i(e^{\frac{qV}{2kT}})}{2\tau_0}.$$

Under forward bias so we can define

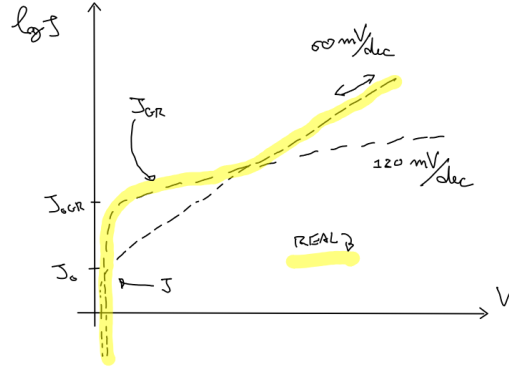
$$J_R = qR_{max}W_d = qW_d \frac{n_i(e^{\frac{qV}{2kT}})}{2\tau_0} \quad (2.20)$$

Under reverse bias $R \simeq -\frac{n_i^2}{2n_i\tau_0} = -\frac{n_i}{2\tau_0}$ and so as for forward bias we can define

$$J_G = -q \frac{n_i}{2\tau_0} W_d \quad (2.21)$$

In general for both cases we can define

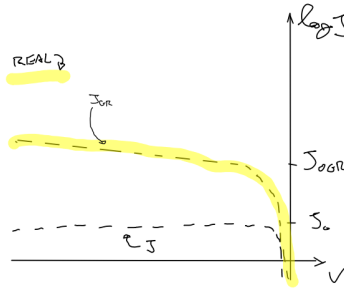
$$J_{GR} = \frac{qn_i}{2\tau_0} W_d (e^{\frac{qV}{2kT}} - 1) = J_{0GR} (e^{\frac{qV}{2kT}} - 1) \quad (2.22)$$



Similar to ideal but J_{0GR} is bigger and we have a factor 2 at the exp so there is a slight difference at very low current.

Note that $J_{0GR} \propto 1/\tau_0$ so is very process dependent and also that $J_{0GR} \propto n_i$ linear dependence on n_i (wrt $J_0 \propto n_i^2$) so at high temperature we recover the ideal diode characteristic.

With reverse bias the current is dominated by J_{RG} and have a slight increase due to the dependence of W_d with V .



2.9.2 High current regime

At high current regime there are 2 problems that create distortions in the ideal characteristic.

High injection regime

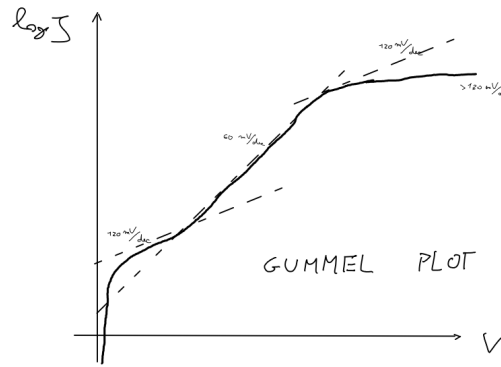
At high current the hypothesis of low injection regime decays so taking p quasi-neutral region we have $n = n_0 + \Delta n \simeq \Delta n$ and $p = p_0 + \Delta n \simeq \Delta n$ so with the law of mass action generalized we obtain $pn = n_i^2 e^{\frac{qV}{kT}} = \Delta n^2$ and so $\Delta n = n_i e^{\frac{qV}{2kT}}$ from this through continuity equation (see 2.6) we get that

$$J \propto n_i e^{\frac{qV}{2kT}} \quad (2.23)$$

so an additional slope of 120mv/dec.

Resistive drops

E_f gradient is no more negligible so we have parasitic resistance due to the law $J_n = n\mu_n \frac{dE_{fn}}{dx}$. To introduce this non ideality we can say that $J = J_0 e^{\frac{qV}{m kT}}$ where m is a factor of non ideality. What it follows is the Gummel plot of the pn junction that include all non idealities.



2.10 Small signal model

The pn junction is, of course, a non linear device if we assume that is polarized at $\bar{V} > 0$ and we change that voltage of δV we are interested in its response. We have 3 small signal parameters: conductance, depletion capacitance and diffusion capacitance.

2.10.1 Conductance

Changing the voltage of δV we have a variation of the current so a conductance that we can calculate as

$$g_m = \frac{\partial I}{\partial V} = \frac{I}{kt/q} \quad (2.24)$$

2.10.2 Depletion capacitance

Changing δV we remove a part of the depletion region as a consequence of majority injected in the junction that neutralize the fixed charges in the DL. We have a variation of the charge stored in the device as a consequence of a variation of the voltage so a capacitance.

We can introduce

$$C_{dep} = \frac{\partial Q_{DL}}{\partial V} = -\frac{\partial}{\partial V}(qN_d x_n) = \frac{\varepsilon_{si}}{W_d} \quad (2.25)$$

The minus sign is place in order to have a positive C and this formula is valid also for non constant doping concentration.

2.10.3 Diffusion capacitance

Also in the quasi-neutral region we have charges stored that change if δV change due to the excess of minority. This capacitance is called diffusion capacitance and is defined as

$$C_{diff} = \frac{\partial Q_{diff}}{\partial V} \quad (2.26)$$

we have therefore define Q_{diff} . Assuming forward bias and so neglecting n_{p0} we can write

$$Q_{diff} = \int_0^{W_p} q\Delta n(x)dx.$$

For a wide base diode we have

$$Q_{diff} = q\Delta n(0) \frac{L_n^2}{L_n} \frac{D_n}{D_n} = J_n \tau_n \quad (2.27)$$

For a narrow base diode

$$Q_{diff} = q\Delta n(0) \frac{W_p^2}{2W_p} \frac{D_n}{D_n} = J_n t_p \quad (2.28)$$

where t_p is defined as electron transit time through the quasi-neutral p region.

It's called like this because from the current equation we can derive that

$$J_n = qD_n \Delta n(0)/W_p = q\Delta n(x)v_{diff} = q\Delta n(0) \frac{W_p - x}{W_p} v_{diff} \text{ from this we obtain } v_{diff} = \frac{D_n}{W_p - x}$$

and from this integrating from 0 to W_p in $dx \frac{1}{v_{diff}}$ we obtain exactly $t_p = \frac{W_p^2}{2D_n}$.

We could have come to the same result by reasoning on the physical situation: in the case of a wide-base diode, since we are in a stationary situation the amount of charge stored in the p-region cannot change, therefore if electrons are entering our region at a given rate, we must remove the same quantity at the same time, which is what the founded relation is saying

$$\frac{Q_{diff}}{\tau_0} = J_n \quad (2.29)$$

Similarly, in a narrow-base diode the electrons entering the region must recombine once they have reached the contact, therefore

$$\frac{Q_{diff}}{t_p} = J_n \quad (2.30)$$

Going back to the diffusion capacitance we have for a wide base diode

$$C_{diff}^{wide} = g_m \tau_n \quad (2.31)$$

and for a narrow base

$$C_{diff}^{narrow} = g_m t_p \quad (2.32)$$

In the end the small signal model is showed in figure.



In reverse bias the modulation of the quasi-neutral change is negligible and so is the diffusion capacitance.

Chapter 3

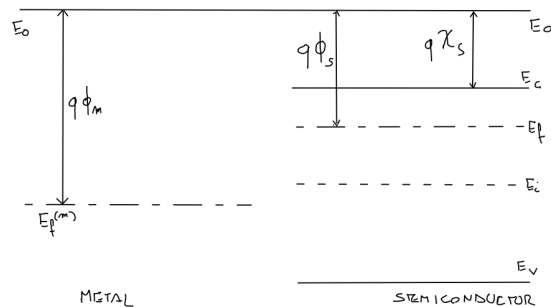
Metal-semiconductor junction

Metal-semiconductor junctions can be divided in 2 categories: ohmic contacts ,that are what we've called "a good contact", and rectifying devices ,that work like diodes. A good contact is a low parasitic resistance device with 2 pin through wich can flow a lot of J with a small V. Rectifying devices let current flow only in one direction, for this type of device is needed a low doped semiconductor and a metal with a proper work function; this type of devices are called Schottky diodes.

3.1 Schottky diode

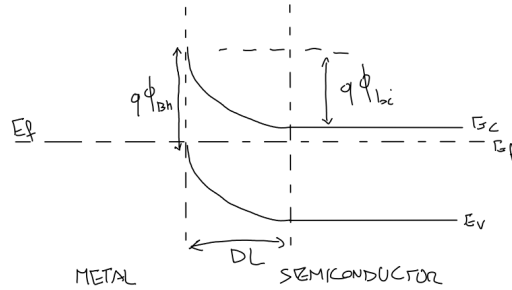
We will study the electrostatic of this device as we've done with diodes. We initially suppose the 2 zones isolated and under thermodynamic equilibrium. Let's take the semiconductor n-doped.

For the metal we're not interested in the conduction or valence band but only in the position of the Fermi level. All type of material's bands are refered to the vacuum level. The distance between the Fermi-level of the metal and the vacuum level E_0 is calle work-function ϕ_m . For silicon we can define the electron affinity that is the distance between the conduction band and the vacuum level χ_s . In this way we can allign the two materials like in figure.



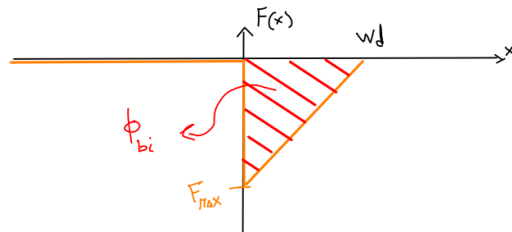
Requirement for a Schottky diode are $E_f^{(m)} < E_f^{(s)}$ and a low doped semiconductor. If

we put the 2 materials together the distance between the difference $q\phi_m - q\chi_s = q\phi_{bn}$ is preserved in the semiconductor the bands goes up to align E_f and we therefore have a built in potential ϕ_{bi} . There is a diffusion process from semiconductor to metal and not in the opposite direction beacuse electrons of metal don't have enough energy.



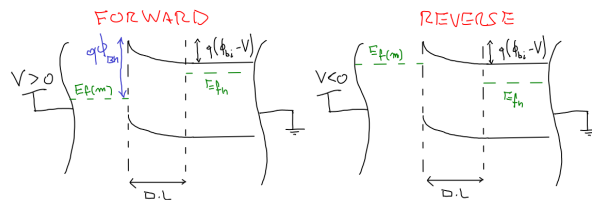
We can also draw a graph of the electric field where we can view the depletion layer and the built in potential as area. This device is an ideal unilateral $p^+ - n$ junction; we have the depletion layer only in the n side. We can recover the expression from the diode

$$W_d = \sqrt{\frac{2\epsilon_{si}}{q} \frac{1}{N_d} \phi_{bi}} = x \quad (3.1)$$



3.1.1 Bias

We will always consider the semiconductor part of the device n-doped and grounded; a voltage will be applied to the metal. As for the pn junction we consider forward bias if the voltage applied is greater than 0 and reverse bias if the voltage applied is less than zero.



Reverse bias

With reverse bias $E_{f(m)}$ becomes higher the depletion layer increases as the total voltage drop over the device.

Forward bias

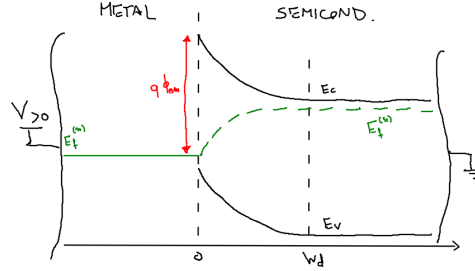
With forward bias $E_{f(m)}$ becomes lower, far from the contact we will have in the semiconductor a quasi-neutral region, near the contact a transition zone with a depletion region. The total voltage drop decreases as the width of the depletion region.

We have two major difference with the pn junction: the flow of electrons from the semiconductor to the metal don't have a minority constrain (the metal is full of electrons) so we will expect a high current but the transport of holes from metal to semiconductor has this

limitation (the semiconductor is n-doped). J_p will be small, negligible with respect to electrons flow.

Metal-semiconductor junction is a majority carrier device we won't deal with minority carrier in current transport phenomena. We will always neglect G-R processes because they are relevant only at low current regime.

3.1.2 Schottky model



We don't know the behaviour of E_{fn} in the depletion layer but we know that in that zone we have the lower concentration of electrons so it can't be flat. Under stationary condition we can say that $J_n = qn\mu_n F + qD_n \frac{dn}{dx} = \text{constant}$ and, as boundary condition, that $n(W_d) = N_d$ $n(0) = N_c e^{\frac{q\phi_{bi}}{kT}}$. F is given $-\frac{qN_d}{\epsilon_{si}}(W_d - x)$ the only parameter we don't know is n and $\frac{dn}{dx}$ so solving the continuity equation for electrons with this boundary conditions we can get that

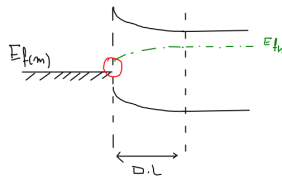
$$J = J_0(e^{\frac{qV}{kT}} - 1) \quad (3.2)$$

that is a relation identical to the pn junction but with a different J_0 .

However this relation does not match the experimental results. This is due to an implicit assumption that we've made using $n(0) = N_c e^{\frac{q\phi_{bi}}{kT}}$ as boundary condition; this happens only if the interface is always at thermodynamic equilibrium.

This model is valid for low mobility semiconductors (not for Si, Ge and GaAs).

3.1.3 Bethe's model



E_{fn} can arrive at the interface higher than $E_{f(m)}$.

We have a very thin interface that is of the order of fractions of nm there we can't describe current transport with drift and diffusion theory because they're dominated by scattering events that occurs in tens of nanometers. We have to use a thermionic transport model.

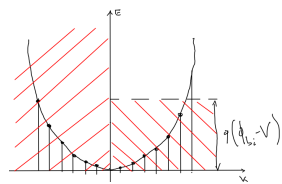
The electrons that pass from semiconductor

to metal are that with an energy greater than $q(\phi_{bi} - V)$

so an energy higher than the potential barrier of the depletion layer.

From energy dispersion relation $E = E_c + \frac{\hbar^2 k_x^2}{2m_x} + \frac{\hbar^2 k_y^2}{2m_y} + \frac{\hbar^2 k_z^2}{2m_z}$ we

define $E_x = \frac{\hbar^2 k_x^2}{2m_x}$ the energy related to x transport and let's take into account only one ellipsoide.



Referring to the interface between the depletion layer and the quasi neutral region, half of the E_x parabola can be neglected because we want electrons that move from right to left (semiconductor to metal). We want also to consider only electrons with energy higher than $q(\phi_{bi} - V)$ so with a $k_x > \bar{k}$ so we can neglect other states.

The equivalent current of this electrons will be

$$J_{s-m}^{(1)} = \sum_{k_x > \bar{k}} 2 \frac{q}{L^3} v_x(k_x) f(k_x, k_y, k_z) \quad (3.3)$$

the 2 factor is a spin correction. Adding a corrective term we can transform the summation into an integral

$$J_{s-m}^{(1)} = \frac{1}{(\frac{2\pi}{L})^3} \int_{\bar{k}_x}^{+\infty} \int_{-\infty}^{+\infty} \int_{-\infty}^{+\infty} \frac{q}{L^3} v_x(k_x) f(k_x, k_y, k_z) dk_x dk_y dk_z \quad (3.4)$$

remembering that $\hbar k_{x,y,z} = m_{x,y,z} v_{x,y,z}$ therefore $dk_{x,y,z} = \frac{m_{x,y,z}}{\hbar} dv_{x,y,z}$, we can change integration variable as

$$J_{s-m}^{(1)} = \frac{2q}{(2\pi)^3} \int_{v_x}^{+\infty} \int_{-\infty}^{+\infty} \int_{-\infty}^{+\infty} v_x f(k_x, k_y, k_z) \frac{m_x m_y m_z}{\hbar^3} dv_x dv_y dv_z \quad (3.5)$$

for f we can use M-B approximation $f \simeq e^{-\frac{E-E_f}{kT}}$ using energy dispersion relation

$$E = E_c + \frac{1}{2} m_x v_x^2 + \frac{1}{2} m_y v_y^2 + \frac{1}{2} m_z v_z^2 \quad (3.6)$$

the M-B equation becomes

$$f \simeq e^{-\frac{E_c - E_{fn}}{kT}} \cdot e^{-1/2 \frac{m_x v_x^2}{kT}} \cdot e^{-1/2 \frac{m_y v_y^2}{kT}} \cdot e^{-1/2 \frac{m_z v_z^2}{kT}} \quad (3.7)$$

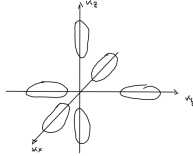
so solving the 3 integral (the first is a gaussian $= \frac{kT}{m_x} e^{-\frac{m_x v_x^2}{kT}}$ second and third $= \sqrt{\frac{2kT\pi}{m_{y,z}}}$) we get

$$J_{s-m}^{(1)} = \frac{4\pi q}{h^3} \sqrt{m_x m_y} (kT)^2 e^{-\frac{\phi_{bn}}{kT}} e^{\frac{qV}{kT}} = A \cdot \sqrt{m_x m_y} T^2 e^{-\frac{\phi_{bn}}{kT}} e^{\frac{qV}{kT}} \quad (3.8)$$

where $A = \frac{4\pi q k^2}{h^3} = 120 \frac{A^2}{cm^2 K^2}$ it's called the Richardson constant.

Taking into account all the ellipsoide we get

$$J_{s-m} = A \frac{2m_t + 4\sqrt{m_t m_l}}{m_0} T^2 e^{-\frac{\phi_{bn}}{kT}} e^{\frac{qV}{kT}} = A^* T^2 e^{-\frac{\phi_{bn}}{kT}} e^{\frac{qV}{kT}} \quad (3.9)$$



with $A^* = A \cdot 2.05$.

From m-s we can say that under th.eq the 2 current must be

equal and that the barrier is constant equal to $q\phi_{bn}$ so $J_{m-s} = A^* T^2 e^{-\frac{\phi_{bn}}{kT}}$.

So finally the total current through the device will be

$$J = A^* T^2 e^{-\frac{q\phi_{bn}}{kT}} (e^{\frac{qV}{kT}} - 1) = J_{0,th} (e^{\frac{qV}{kT}} - 1) \quad (3.10)$$

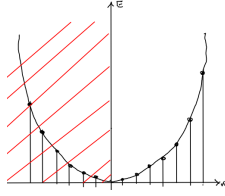
ϕ_{bn} it's a crucial parameter for current flow in metal semiconductor junction. We have a $J_{0,th} \simeq 10^5 A/cm^2$ orders of magnitude higher with respect to the pn junction, a turn on voltage of 0.3-0.4 V and also a greater reverse bias current due to higher J_0 .

This model is valid for high mobility semiconductors.

3.1.4 Universal model

We can connect the two models in an universal one.

Starting from Schottky model we can use his assumption of $J_n = qn\mu_n F + qD_n \frac{dn}{dx} = const$ and $n(W_d) = N_d$ but we have to change $n(0)$. We can say something about $J_n(0)$ as the current density without scattering.



We can calculate that term using energy dispersion relation but because we are at the interface we will take all the left state of the parabola (we don't have a barrier) so we get

$$J_n(0) = A^* T^2 e^{-\frac{E_c - E_{fn}(0)}{kT}} \quad (3.11)$$

that is the correct boundary condition. If we multiply and divide this expression by N_c we obtain

$$J_n(0) = A^* T^2 \frac{n(0)}{N_c} \quad (3.12)$$

this for the electron flow from semiconductor to the metal. For the opposite direction we use the th.eq. condition and we get

$$J_n(0) = A^* T^2 \frac{n_0}{N_c} \quad (3.13)$$

with n_0 electron concentration at the interface under th.eq. So the final boundary condition is

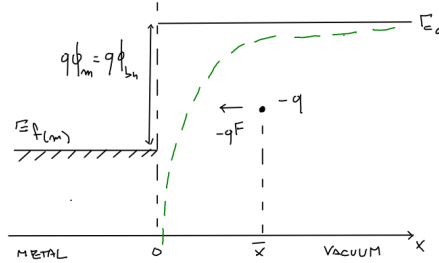
$$J_n(0) = \frac{A^* T^2}{N_c} [n(0) - n_0] \quad (3.14)$$

We are using a drift-diffusion approach with thermionic boundary condition.

Solving this system we get an expression valid for all semiconductors that can be simplified in the 2 models depending on what type of semiconductor we have.

If mobility is large than it's easy to move electrons but difficult to remove them from the interface that becomes the bottom neck of the system. With low mobility it's difficult to move electrons but easy to remove them from the interface so they don't pile up there.

3.1.5 Schottky effect



The Schottky effect is a pure electrostatic effect that takes place in the Bethe's model.

To study this effect we start from a metal-vacuum "junction" placing in the vacuum a single electron at a certain distance \bar{x} . We have an electrostatic induction at the surface of the metal that attracts the electron in the vacuum near the surface. In order to calculate the electric field that attracts the single electron we can use the image method placing a positive charge $+q$ at $-\bar{x}$ and removing the metal. From this assumption we get

$$-qF = \frac{1}{4\pi\epsilon_0} \frac{-q^2}{(2\bar{x})^2} \quad (3.15)$$

and so the electric field

$$F = \frac{q}{16\pi\epsilon_0 x^2} \quad (3.16)$$

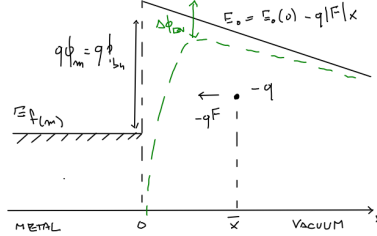
from which we can calculate, integrating both parts of the equation from x to $+\infty$, the potential as

$$\phi(x) = \phi(+\infty) + \frac{q}{16\pi\epsilon_0 x} \quad (3.17)$$

Multiplying for $-q$ we can obtain the energy

$$E_0(x) = E_0(+\infty) - \frac{q^2}{16\pi\epsilon_0 x} \quad (3.18)$$

and so the profile in green in the graph above.



If we consider that in the vacuum there is a constant electric field (and so $E_0(x) = E_0(0) - q|F|x$) like in figure because the system is linear we obtain that

$$E_0(x) = E_0(0) - q|F|x - \frac{q^2}{16\pi\epsilon_0 x} \quad (3.19)$$

and the behaviour in green in figure. We have change of the peak and so of the barrier that block our electrons. The Δ of the barrier is called Schottky barrier lowering.

We can calculate the new peak deriving by dx the $E_0(x)$ function finding the x_{max} obtaining the energy at that point

$$E_0(x_{max}) = E_0(0) - \sqrt{\frac{q^3|F|}{4\pi\epsilon_0}} \quad (3.20)$$

So the difference in the barrier is $\Delta\phi_{bn} = \sqrt{\frac{q^3|F|}{4\pi\epsilon_0}}$.

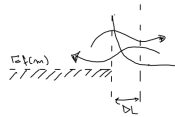
Now let's apply this effect on our metal semiconductor junction: when an electron travels through the depletion layer from the semiconductor to the metal we have a barrier lowering of $\Delta\phi_{bn} = \sqrt{\frac{q^3|F_{max}|}{4\pi\epsilon_{Si}}}$ (we place F_{max} because the maximum effect we have is with the max F and the narrower distance).

In our device we have a change of the J-V characteristic

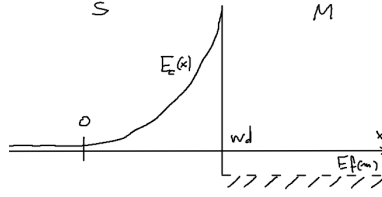
$$J = A^* T^2 e^{\frac{-q(\phi_{bn} - \Delta\phi_{bn})}{kT}} (e^{\frac{qV}{kT}} - 1) \quad (3.21)$$

that creates an increment of J_0 and 2 opposite behaviour for reverse and forward bias: with $V < 0$ J_0 increases increasing $|V|$, with $V > 0$ J_0 decrease this due to the dependence of $\Delta\phi_{bn} \propto \sqrt{F_{max}} \propto V_{rv-bias}$.

3.2 Ohmic contact



In order to have an ohmic contact we need a high doped semiconductor. With N_d very high the depletion layer becomes narrower and increasing the doping concentration we arrive at a condition when there is a strong factor of J due to quantum-mechanical tunneling. That process does not depend on the type of bias so we don't have anymore a rectifying behaviour.



Taking into account the figure as reference system from the studied pn junction we know the behaviour of $E_c(x) = \frac{q^2 N_d}{2\epsilon_{Si}} x^2$ so we can calculate T ,transparency coefficient as

$$T = e^{-2 \int_0^{W_d} \text{Im}\{E_c(x)\} dx} = e^{-2 \int_0^{W_d} \sqrt{\frac{2m^* (E_c - E)}{\hbar^2}} dx} \quad (3.22)$$

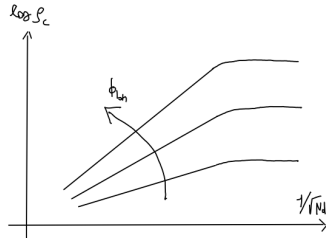
we have to remember that in this case m^* is the effective mass for tunneling process. So if we consider $E = E_f$ (taken E_f as reference the barrier is $E_c = \frac{q^2 N_d}{2\epsilon_{Si}} x_n^2$)

$$T = e^{-2 \int_0^{W_d} \sqrt{\frac{2m^* E_c}{\hbar^2}} dx} = e^{-2 \sqrt{\frac{2m^*}{\hbar^2}} \sqrt{\frac{q^2 N_d}{2\epsilon_{Si}}} W_d^2 / 2} \quad (3.23)$$

That substituiting W_d with its expession we get

$$T = e^{-2 \sqrt{\frac{2m^*}{\hbar^2}} \sqrt{\frac{q^2 N_d}{2\epsilon_{Si}}} \frac{2\epsilon_{Si}}{q N_d} (\phi_{bi} - V)} = e^{-q \frac{(\phi_{bi} - V)}{E_{00}}} \quad (3.24)$$

where $E_{00} = q \frac{\hbar \sqrt{N_d}}{2 \sqrt{m^* \epsilon_{Si}}}$

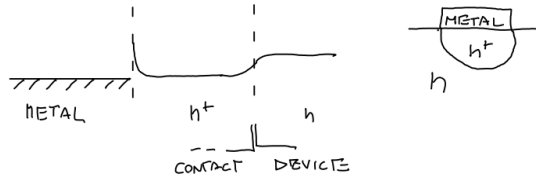


One important parameter of this device is the contact resistivity defined as

$$\rho_c = \left(\frac{\partial J}{\partial V} \right)^{-1} \Big|_{V=0} = \frac{E_{00}}{q} e^{q \phi_{bi} / E_{00}} \quad (3.25)$$

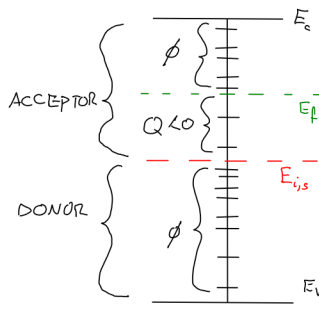
This parameter depends on the barrier high and on $\sqrt{N_d}$. In the graph shows the $\log(\rho_c) - 1/\sqrt{N_d}$ dependance. It's a straight line until the concentration becomes too low and so tunneling effect is no more relevant.

To achive large current flow we need to perturbe only al little bit the device so it stays always near thermodynamic equilibrium. The two figures below show how a contact is done in a device.



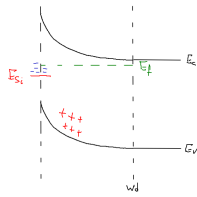
3.3 Interface states

We've always considered Si as a periodic infinite cristal but in metal-semiconductor junction we have the interface that interrupts the sequence of atoms. Some atoms of Si can't share all theyr 4 valence electrons creating some dangling bonds.



Electrons remains localize close to they silicon atoms this creates spurius energy level at the interface. In the bulk region electrons and holes are only in the conduction band or in the valence band but at the interface can stay in a lot of states between this two bands. The spurious states in the upper part of the bandgap have an acceptor behaviour (negatively charged when filled and neutral when empty) the others in the bottom part have a donor behaviour (neutral when filled and positively charged when empty). The energy that divide this two type of states is the E_{is} .

All states below E_f will be filled all the other states empty. So the previous band-diagram is incoherent with the Gauss'law since we have some exposed charge and no band banding.



We have a negative charge so $\phi < 0$ the bands band upward and the distance $E_f - E_{is}$ becomes narrower. The bands banding create a depletion region that expose a positive charge equal to the interface states' charge.

The distance between $E_c - E_f$ is not set only by doping concentration but also from interface states.

We define interface state density $N_{is} [cm^{-2}eV^{-1}]$ in order to find the total charge introduced by the interface

$$|Q_{is}| = N_{is}(E_f - E_{is})q \quad (3.26)$$

The distance $E_c(0) - E_{is} \simeq E_{gap}/2$ so writing $\Delta E_{is} = E_c(0) - E_{is} \simeq E_{gap}/2$ we can say that

$$|Q_{is}| = N_{is}[\Delta E_{is} - (E_c(0) - E_f)]q \quad (3.27)$$

We know from the analysis of the pn junction that the charge in the depletion leyer is

$$Q_{dep} = qN_dW_d = \sqrt{2\varepsilon_{si}qN_d \frac{E_c(0) - E_c(W_d)}{q}} \quad (3.28)$$

where the last term is the voltage drop in the depletion layer.

For Gauss law this 2 terms have to be equal so solving the equation we get the level of the conduction band at the interface

$$E_c(0) = \Delta E_{is} + \frac{\varepsilon_{si}N_d}{q^2N_{is}^2} - \sqrt{\left(\frac{\varepsilon_{si}N_d}{q^2N_{is}^2}\right)^2 + \frac{2\varepsilon_{si}N_d}{q^2N_{is}^2}(\Delta E_{is} - E_c(W_d))} \quad (3.29)$$

This effect changes the barrerier hight and so theflow of current throught the device. ϕ_{bn} becomes strongly dependent on N_{is}

3.3.1 Limit cases

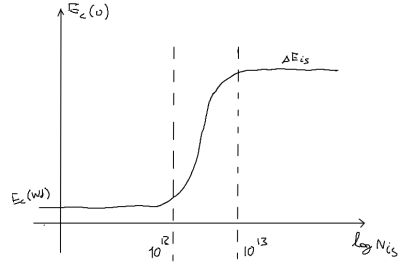
Starting from the equation $|Q_{is}| = Q_{dep}$ we have 2 limit cases.

$N_{is} = 0$ in this case $E_c(0) = E_c(W_d)$ so we don't have a band banding we restore the ideal case.

$N_{is} \rightarrow +\infty$ in this case we notice that the first term has to be finite and so $\Delta E_{is} - (E_c(0) - E_{is})$ has to be zero that means that $E_c(0) = E_f + \Delta E_{is}$.

This case means we are moving E_f up to E_{is} that is totally indipendent from doping concentration but depends only from the interface states. This condition is called "Fermi level pinning at the surface".

The plot of $E_c(0) - \log(N_{is})$ make a transition between $10^{12} - 10^{13}$ as order of magnitude.



3.4 Considerations

3.4.1 M-S junction but with $\phi_m > E_f$

Why this structure is futile, what are the critical points?

Chapter 4

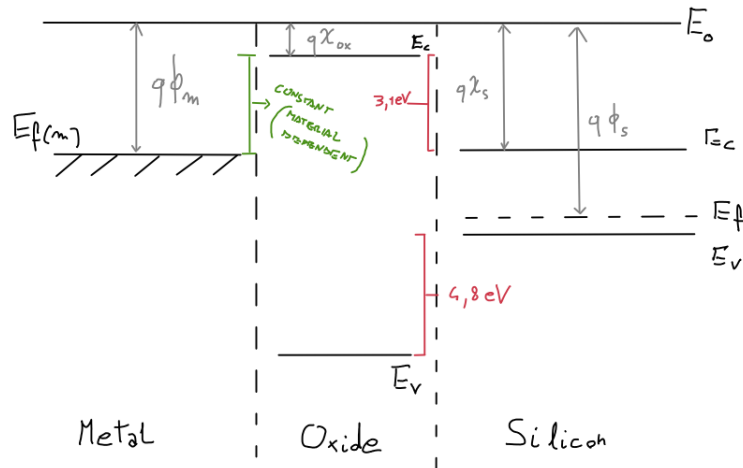
MOS capacitor

We start our analysis with a 1D device, we will consider the substrate a monocrystal of constant p-doped silicon.

We will consider for oxide SiO_2 that has a high energy gap ($\simeq 8-9\text{eV}$), a low concentration of free carriers, a large resistivity, a reasonably low concentration of spurious defect ($\simeq 10^{10}\text{cm}^{-3}$) but a low dielectric constant ($\simeq 3.9$). This last propriety is the cause why recently SiO_2 is being substituted with high-k materials.

In our analysis we will consider the dielectric ideal (this means we have to solve only the Poisson eq. for the electrostatic beacuse there will be no current flow) and as gate material a metal.

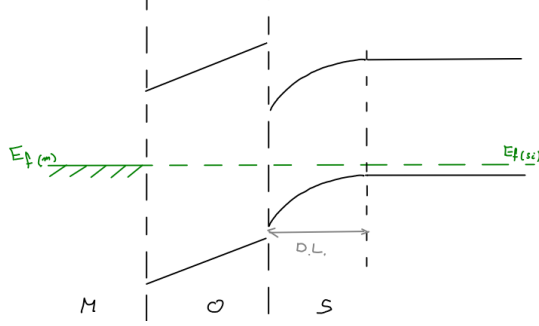
4.1 Working regimes



We start considering the 3 material isolated from each other under th.eq.

We will refer $E_{f(m)} \simeq E_c^{Si}$. we have also to introduce the vacuum level and so electron affinity for oxide and silicon, metal work function, and silicon work function. From this data we can say that the metal we need is Al in order to maintain $E_{f(m)} \simeq E_c^{Si}$.

We also underlined in red the potential barrier created by the oxide for holes and electrons.



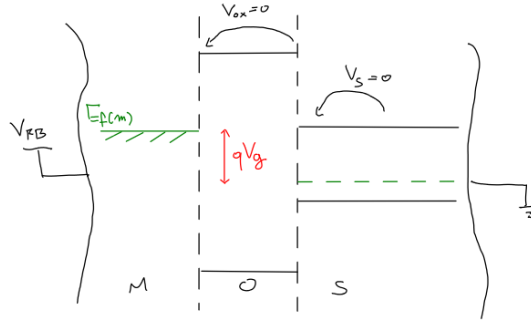
We put the 3 materials in contact after a while we will have a single Fermi-level all over the device and we can say that far from the contact p-Si will be at equilibrium. $E_{f(m)}$ will move downwards together with E_c^{ox} since the distance $E_{f(m)} - E_c^{ox}$ is constant (material dependent) as E_{gap}^{ox} . We have discontinuity of F, for Gauss law $\epsilon_{ox} F_{ox} = \epsilon_{Si} F_{Si} \rightarrow F_{ox} = 3F_{Si}(0)$. We have a linear band bending in the oxide for the hp of ideality of the dielectric (no charge distribution inside) and a parabolic band

bending (that means a linear F) in the Si.

We have 2 voltage drops over the silicon and over the metal that define $V_s + V_{ox} = \phi_{bi}$. If we apply a $V > 0$ at the gate we push $E_{f(m)}$ downwards creating a higher band bending both in oxide and silicon, this band bending will increase both V_{ox} and V_s so assuming that the bulk keeps th.eq we can write the following equation

$$V_G + \phi_{bi} = V_s + V_{ox} \quad (4.1)$$

4.1.1 Flat band regime



If we apply $V_G = -\phi_{bi}$ from the previous equation we have that $V_s = V_{ox} = 0$ and a separation $E_{f(m)} - E_{f(Si)} = qV_G$. This is the so called Flat-band condition of the mos capacitor

$$V_{FB} = -\phi_{bi} \quad (4.2)$$

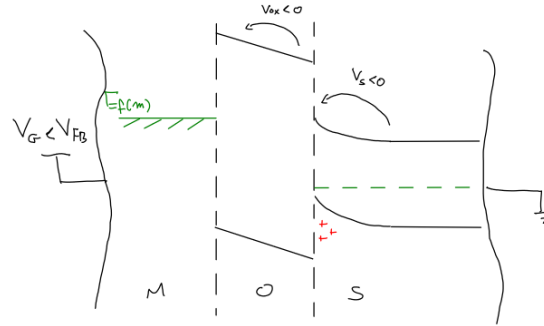
Is defined as the voltage to apply at the gate to have all bands flat. now we can re-write the balance of voltages as

$$V_G - V_{FB} = V_s + V_{ox} \quad (4.3)$$

V_{fb} can be found considering complete ionization as

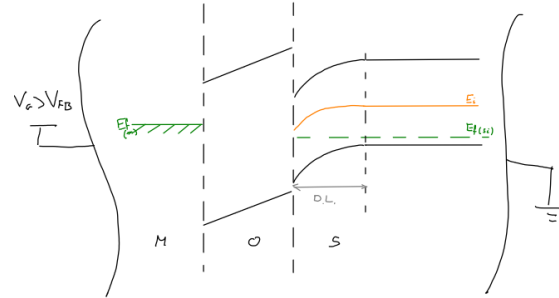
$$V_{FB} = \frac{kT}{q} \ln\left(\frac{N_a}{n_i}\right) + \frac{E_g}{2} \quad (4.4)$$

4.1.2 Accumulation regime



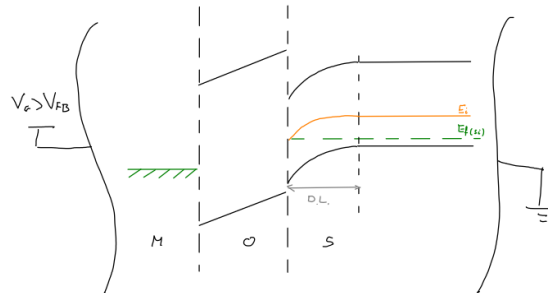
If $V_G < V_{FB}$ bands bend upwards we have more hole concentration at the interface between Si-Ox than the doping concentration. This is called the accumulation regime.

4.1.3 Depletion regime



With $V_G > V_{FB}$ we have in silicon a depletion region so we are in the depletion regime of the MOS capacitor.

4.1.4 Weak inversion condition



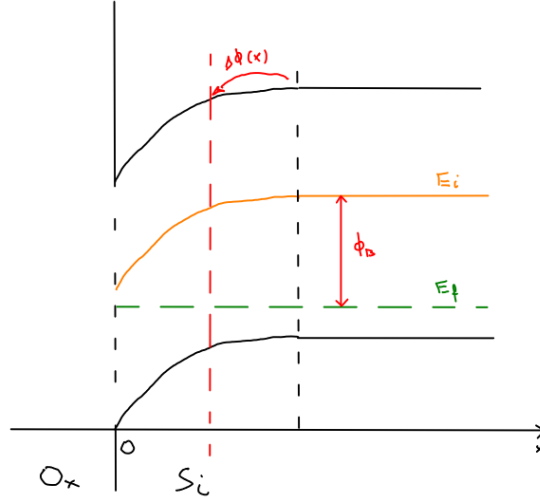
If we further increase $V_G \gg V_{FB}$ we arrive at the condition that the intrinsic Fermi level at the surface reaches the Fermi level ($E_f = E_i$).

From now on if we slightly increase the voltage we will have more electrons than holes at the interface. This is the condition for weak inversion condition.

4.1.5 Strong inversion regime

If we continue to increase the voltage applied we will reach the strong inversion regime that is characterized by $(E_i - E_f)|_{interface} = -(E_i - E_f)|_{bulk}$ so the concentration of electrons at the interface is equal to the doping concentration in the bulk.

4.2 Electrostatics



We have to solve the Poisson equation $\frac{d^2\phi}{dx^2} = -\frac{q}{\epsilon_{Si}}(p - n - N_a^-)$ only in the substrate.

We define $\phi_B = (E_f - E_i)_{bulk}/q = [E_f = 0] = -\frac{kT}{q} \ln(N_a/n_i)$ the electrostatic potential of the bulk far away from the interface and we take E_f that is constant as the reference energy level 0. We introduce also $\Delta\phi(x) = \phi(x) - \phi_B$ that is the change of the electrostatic potential wrt the bulk; $\Delta\phi(W_d) = 0$ and $\Delta\phi(0) = V_s$.

Now we have to write $p - n - N_a^-$ as function of $\phi(x)$.

For electrons we can say that $n = n_i e^{(E_f - E_i)/kT}$ if we multiply and divide by q we get $n = n_i e^{q\phi(x)/kT}$ same for holes as $p = n_i e^{-q\phi(x)/kT}$. Electrons and holes in the bulk are $n_0 = n_i e^{q\phi_b/kT}$ and $p_0 = n_i e^{-q\phi_b/kT}$. From this 4 equation we can write that

$$n = n_0 e^{q\Delta\phi/kT} \quad p = p_0 e^{-q\Delta\phi/kT} \quad (4.5)$$

In the bulk we can say that $p_0 = n_0 + N_a$ so

$$N_a = p_0 - n_0 \quad (4.6)$$

Now Poisson equation becomes

$$\frac{d^2\phi}{dx^2} = -\frac{q}{\epsilon_{Si}}(p_0 e^{-q\Delta\phi/kT} - n_0 e^{q\Delta\phi/kT} - p_0 + \frac{n_i^2}{p_0}) \quad (4.7)$$

Until now the only approximation we have made is the M-B. Now we consider the complete ionization approximation $p_0 \simeq N_a$. And we make a change of variable

$$\frac{d^2\phi}{dx^2} = -\frac{q}{\epsilon_{Si}}(N_a e^{-q\Delta\phi/kT} - \frac{n_i^2}{N_a} e^{q\Delta\phi/kT} - N_a + \frac{n_i^2}{N_a}) \quad (4.8)$$

$$d\left(\frac{d\phi}{dx}\right) = -\frac{q}{\varepsilon_{Si}} \left(N_a e^{-q\Delta\phi/kt} - \frac{n_i^2}{N_a} e^{q\Delta\phi/kt} - N_a + \frac{n_i^2}{N_a} \right) dx \quad (4.9)$$

$$\frac{d\phi}{dx} d\left(\frac{d\phi}{dx}\right) = -\frac{q}{\varepsilon_{Si}} \left(N_a e^{-q\Delta\phi/kt} - \frac{n_i^2}{N_a} e^{q\Delta\phi/kt} - N_a + \frac{n_i^2}{N_a} \right) dx \frac{d\phi}{dx} \quad (4.10)$$

Now we integrate one time this expression form $\Delta\phi$ to 0. The first member is like $f(x)f'(x)$ so the result is $-1/2(\frac{d\phi}{dx})^2$. Integrating also the second member and gathering the common terms the equation we get

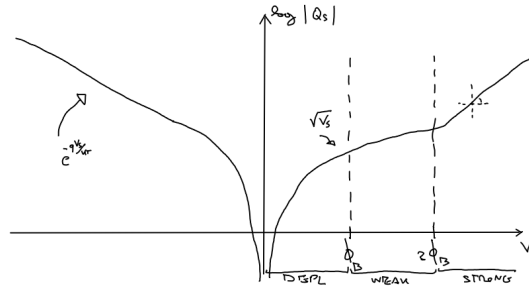
$$\left(\frac{d\Delta\phi}{dx}\right)^2 = \frac{2kTN_a}{\varepsilon_{Si}} \left(e^{-q\Delta\phi/kt} + \frac{q\Delta\phi}{kT} - 1 + \frac{n_i^2}{N_a^2} \left(e^{q\Delta\phi/kt} - \frac{q\Delta\phi}{kT} - 1 \right) \right) = F^2(x) \quad (4.11)$$

For Gauss law $F(0) = -\frac{Q_s}{\varepsilon_{Si}}$ (and also that $\Delta\phi(0) = V_s$) from this relation and the previous equation we get

$$Q_s = \pm \sqrt{2kTN_a\varepsilon_{Si}} \left(e^{-qV_s/kt} + \frac{qV_s}{kT} - 1 + \frac{n_i^2}{N_a^2} \left(e^{qV_s/kt} - \frac{qV_s}{kT} - 1 \right) \right)^{1/2} \quad (4.12)$$

We already know the total charge in the substrate for all working regimes.

4.2.1 Dominant terms in the solution of Poisson equation



To better understand this formula let's analyse all working regime separately and draw a $\log|Q_s| - V_s$ graph.

In accumulation regime when $V_s < 0$ we have that $Q_s \simeq \sqrt{2kTN_a\varepsilon_{Si}} e^{-\frac{qV_s}{2kT}}$. So in the graph we see a straight line dependence. We can say that the term

$$e^{-\frac{qV_s}{kT}} \rightarrow h_{sub} \quad (4.13)$$

in the solution of the Poisson equation is the term that takes into account for hole concentration in the substrate.

In the depletion regime $0 < V_s < 2|\phi_b|$ we have to consider two dominant term: $\frac{qV_s}{kT}$ and $\frac{n_i^2}{N_a^2} e^{\frac{qV_s}{kT}}$. If we evaluate the second term at $2|\phi_b|$ we get 1 so it's negligible and therefore the first term is predominant. In this regime

$$Q_s \simeq -qN_a \sqrt{\frac{2\varepsilon_{Si}}{q} \frac{1}{N_a} V_s} = -qN_a W_d \quad (4.14)$$

that is the charge of the depletion layer.

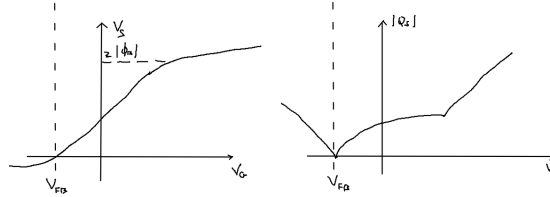
In strong inversion $Q_s \simeq \sqrt{2kTN_a\epsilon_{si}} \frac{n_i}{N_a} e^{\frac{qV_s}{2kT}}$ so we can say that the term

$$\frac{n_i^2}{N_a^2} e^{\frac{qV_s}{kT}} \rightarrow e_{sub} \quad (4.15)$$

in the solution of the Poisson equation is the term that takes into account electrons in the substrate.

4.2.2 Total charge in function of gate bias

We want $Q(V_g)$ not $Q(V_s)$; to have that expression we need to remember that $V_g - V_{fb} = V_s + V_{ox}$ but we can write $V_{ox} = F_{ox}t_{ox} = \frac{\epsilon_{si}F_{si}}{\epsilon_{ox}}t_{ox} = -Q(V_s)/C_{ox}$ so $V_g - V_{fb} = V_s - \frac{Q_s}{C_{ox}}$ using this expression and $Q_s = Q_s(V_s)$ we can get what we want. We will plot also the 2 graphs $V_s - V_g$ and $|Q_s| - V_g$.



We will take as reference point the flat band condition where $Q_s = 0$ and $V_s = 0$.

For $V_s < 0$ we said that $Q_s \simeq \sqrt{2kTN_a\epsilon_{si}} e^{-\frac{qV_s}{2kT}}$ so we get that

$$V_g - V_{fb} = V_s - \frac{\sqrt{2kTN_a\epsilon_{si}}}{C_{ox}} e^{-\frac{qV_s}{2kT}} \quad (4.16)$$

we can neglect V_s beacuse it's negligible wrt the exponential term so we get

$$V_s \simeq -\frac{2kT}{q} \ln \left(\frac{C_{ox}(V_{fb} - V_g)}{\sqrt{2kTN_a\epsilon_{si}}} \right) \quad Q_s \simeq C_{ox}(V_{fb} - V_g) \quad (4.17)$$

a small variation of V_g let V_s move not so much due to the exponential increase of the charge in the bulk and a consequent big field in the oxide; we are not far from a metal plate capacitor.

For $0 < V_s < \phi_b$ we get that $Q_s \simeq \sqrt{2qN_a\epsilon_{si}V_s}$ so we get the following equation (that we don't solve)

$$V_g - V_{fb} = V_s + \frac{\sqrt{2qN_a\epsilon_{si}V_s}}{C_{ox}} \quad (4.18)$$

For weak inversion $\phi_b < V_s < 2\phi_b$ we can consider both dominants terms getting the following equation

$$V_g - V_{fb} = V_s + \frac{\sqrt{2\epsilon_{si}kTN_a}}{C_{ox}} \left(\frac{qV_s}{kT} + \frac{n_i^2}{N_a^2} e^{qV_s/kT} \right)^{1/2} \quad (4.19)$$

$$V_g - V_{fb} \simeq V_s + \frac{\sqrt{2\epsilon_{si}kTN_a}}{C_{ox}} \sqrt{\frac{qV_s}{kT}} \left(1 + \frac{n_i^2}{2N_a^2} e^{qV_s/kT} \frac{kT}{qV_s} \right) \quad (4.20)$$

using Taylor expansion we get an exponential dependance on V_g of the e charge (that is the second term). Form this dependance we will get the sub-th current of the mos capacitor.

For strong inversion we get

$$V_g - V_{fb} = V_s + \frac{\sqrt{2\varepsilon_{si}kTN_a}}{C_{ox}} \frac{n_i}{N_a} e^{qV_s/2kT} \quad (4.21)$$

remembering that $\frac{n_i^2}{N_a^2} e^{q2|\phi_b|/kT} = 1$ we can say that $\frac{n_i}{N_a} = e^{-q2|\phi_b|/2kT}$ so we can write that

$$V_g - V_{fb} = V_s + \frac{\sqrt{2\varepsilon_{si}kTN_a}}{C_{ox}} e^{\frac{q(V_s - 2|\phi_b|)}{2kT}} \quad (4.22)$$

So we get V_s

$$V_s = 2|\phi_b| + \frac{2kT}{q} \ln \left(\frac{C_{ox}(V_g - V_{fb} - V_s)}{\sqrt{2\varepsilon_{si}kTN_a}} \right) \quad (4.23)$$

and making a rough approx of $V_s \simeq 2|\phi_b|$, due to the log dependance, also Q_s

$$Q_s = -C_{ox}(V_g - V_{fb} - V_s) \simeq -C_{ox}(V_g - V_{fb} - 2|\phi_b|) \quad (4.24)$$

The approximation means that entering in strong inversion we get a maximum depletion layer and a maximum depletion charge

$$W_d^{max} = \sqrt{\frac{2\varepsilon_{si}}{qN_a} 2|\phi_b|} \quad Q_{dep}^{max} = -\sqrt{2\varepsilon_{si}qN_a 2|\phi_b|} \quad (4.25)$$

we increase the charge of electrons not that of the depletion layer.

The V_g at which we enter in the strong inversion is $V_g - V_{fb} = 2|\phi_b| + \frac{|Q_{dep}^{max}|}{C_{ox}}$ that is called threshold voltage of the mos capacitor that is

$$V_t = V_{fb} + 2|\phi_b| + \frac{|Q_{dep}^{max}|}{C_{ox}} \rightarrow Q_{inv} = Q_s - Q_{dep}^{max} = -C_{ox}(V_g - V_t) \quad (4.26)$$

4.3 Small signal capacitance

We want to study the small signal capacitance of the MOS capacitor that is a non linear device so we want $C_g = -\frac{dQ_s}{dV_g}$ the change of charge over the change of voltage.

We can guess the behaviour of C_g using the expression $V_g - V_{fb} = V_s - Q_s/C_{ox}$ and calculating the derivative wrt $d(-Q_s)$ we get

$$\frac{dV_g}{d(-Q_s)} = \frac{dV_s}{d(-Q_s)} + \frac{1}{C_{ox}} \quad (4.27)$$

that is

$$\frac{1}{C_g} = \frac{1}{C_s} + \frac{1}{C_{ox}} \quad (4.28)$$

The total gate capacitance can be expressed by the series of 2 capacitive terms one fixed (C_{ox}) one variable (that is the substrate capacitance C_s). From this we know that C_g has an upper limit of C_{ox} .

Let's analyse the small signal capacitance in the various regime.

4.3.1 in accumulation regime

We derivate the charge of the accumulation region obtaining

$$C_s = \sqrt{2kTN_a\epsilon_{si}} e^{-\frac{qV_s}{2kT}} \frac{q}{2kT} = Q_s / \frac{2kT}{q} \quad (4.29)$$

Knowing $Q_s(V_g)$ we get

$$C_s = \frac{C_{ox}(V_{fb} - V_g)}{2kT/q} \quad (4.30)$$

This is $\gg C_{ox}$ if $V_{fb} - V_g \gg 2kT/q$. So from flat band to minus infinite the capacitance increases and becomes similar to C_{ox} . We are close to a metal plate capacitor.

4.3.2 in flat band condition

We have to include in the Q expression both electrons and holes so

$$Q_s = \sqrt{2kTN_a\epsilon_{si}} \left(e^{\frac{-qV_s}{kT}} + \frac{qV_s}{kT} - 1 \right)^{1/2}.$$

If we make the Taylor expansion of the exponential term around 0 we get $Q_s = -V_s \sqrt{\frac{\epsilon_{si}q^2N_a}{kT}}$ so

$$C_s = \frac{d(-Q_s)}{dV_s} = \frac{\epsilon_{si}}{\sqrt{\frac{\epsilon_{si}kT}{q^2N_a}}} = \frac{\epsilon_{si}}{L_D} \quad (4.31)$$

we can recognise the Dybae lenght in the expresion we can interpretate this result as this ; the holes (majority) screen a perturbation of the electric field form the gate like a step increase of doping concentration.

This capacitance and the oxide capacitance are comparable.

4.3.3 in depletion regime

In depletion regime we have a charge $Q_s = -\sqrt{2\epsilon_{si}qN_aV_s}$ that is the usual expression for the charge in a depletion layer. From the well known reation $C = \epsilon_{si}/W_d$ we get

$$C_g = C_{ox} / \sqrt{1 + 2C_{ox}^2 \frac{V_g - V_{fb}}{\epsilon_{si}qN_a}} \quad (4.32)$$

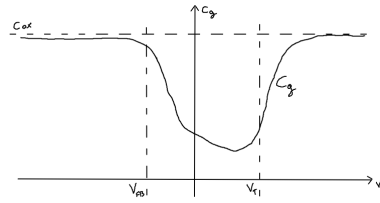
This capacitance decrease quickly near the flat band condition beacuse the contribution related to holes disappears over a few kT/q .

4.3.4 in strong inversion

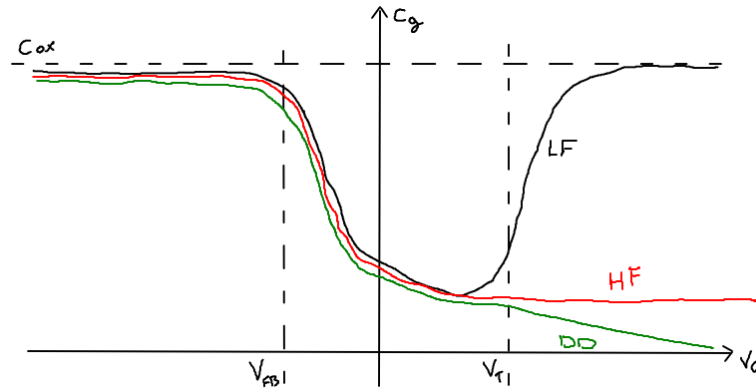
We have the charge $Q_s = \sqrt{2\epsilon_{si}kTN_a} \frac{n_i}{N_a} e^{\frac{qV_s}{2kT}}$ so making the derivate we reach

$$C_s = \frac{|Q_s|}{2kT/q} = C_{ox} \frac{(V_g - V_{fb} - 2|\phi_b|)}{2kT/q} \quad (4.33)$$

Increasing V_g we get a larger capacitance we reach a condition similar to a metal plate capacitance.



4.4 Frequency regimes



Let's look more closely to the substrate during the different regimes when we apply a small signal to the gate.

In accumulation regime

$\bar{V}_g < V_{fb}$ if we move the gate of $\delta V_g > 0$ we are removing h from the silicon surface to the substrate. Vice-versa with $\delta V_g < 0$ we move h from the substrate to the silicon surface. This is a modulation of majority carriers concentration so it happens in a very short time in the order of the dielectric relaxation time.

In weak inversion

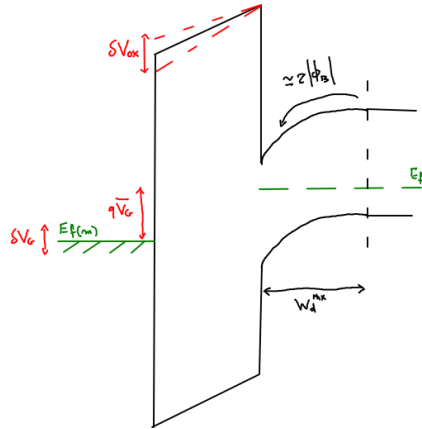
$V_{fb} < \bar{V} < V_t$ we have a depletion region with a certain voltage drop V_s and an exposed negative charge at the surface.

With a $\delta V_g > 0$ we slightly increase the width of the depletion layer so we are removing holes from the edge of the depletion layer to the substrate. With $\delta V_g < 0$ we reduce the depletion layer so we add h from the substrate to the depletion layer to neutralize the exposed charge. Also here we modulate the majority carrier so this is a process that have as time constant the dielectric relaxation time.

Strong inversion

Depletion layer at the maximum expansion at the silicon surface we have a lot of electrons. Applying δV_g we modulate e concentration this electrons cannot come from the contact that exchange only majority they have to be created by generation processes.

4.4.1 Low frequency regime



The time constant

for the generation process in strong inversion can be extracted from the generation current $J_g = q \frac{n_i}{2\tau_0} W_d^{max}$ that is the total current that can be created per unit time per unit area. The charge of the depletion layer is $Q_{dep} = q N_a W_d^{max}$ the time for generate this charge is

$$\tau_g = \frac{Q_{dep}}{J_g} = 2\tau_0 N_a / n_i \quad (4.34)$$

τ_g is technology

dependent and very big in the order of seconds.

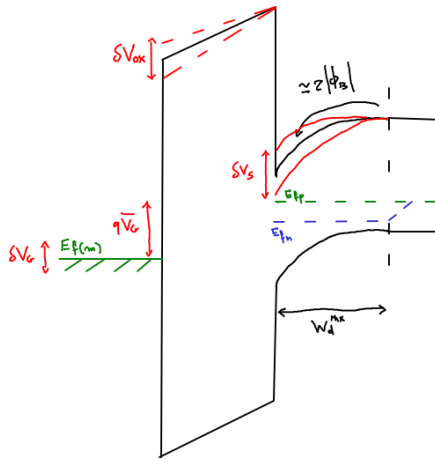
Only if the

signal has a frequency much lower than τ_g ($f < 1Hz$) we have the ideal characteristic seen before.

Looking at the band diagram a movement of δV_g

moves $E_{f(m)}$ upwards or downwards. With a $\delta V_g > 0$ we have to increase the total voltage drop but the dependance with V_{sub} is very weak (logaritmik dependance) so $\delta V_s \simeq 0$ and we modulate only the voltage drop over the oxide (this under charge sheet approximation, that we will see in next chapter, since we're breaking the continuity law of the electric field $F_{ox}\epsilon_{ox} = F_{Si}\epsilon_{Si}$) $\delta V_g \simeq \delta V_{ox}$

4.4.2 High frequency regime



For signals with high frequency

($f > 1Hz$) we cannot change electron concentration

so we can only add or remove holes at the substrate making the depletion layer bigger or smaller.

The graph

of C_g remains constant form the threshold voltage on.

The total capacitance depends

on the frequency of the small signal we are applying.

Here the modulation of δV_g can't modulate

the electron concentration at the surface of silicon.

There is a modulation of the depletion layer so δV_s but

for the continuity of the electric field also δV_{ox} have to change in a comparable manner. With the downwards

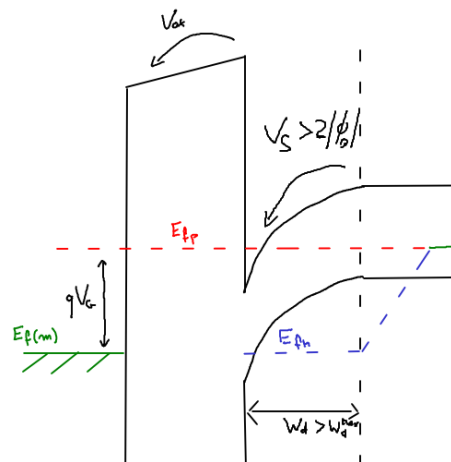
band banding we have to keep constant the distance with E_{fn} with the conduction band so our substrate

is no longer at th.eq. This triggers GR processes

that tends to move the system back in the th.eq of low

frequency. E_{fn} is constant over the depletion layer and merges with E_{fp} in the quasi neutral region of the device. We have a flow of electrons from the substrate to the surface similar to the pn-j reverse current.

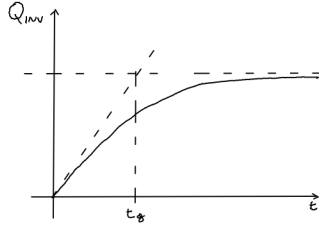
4.4.3 Deep depletion



If we consider a step increase of the gate voltage form 0 to $\bar{V}_g > V_t$ we don't give the time to the system to create electrons so we get a super wide depletion layer

$W_d \gg W_d^{max}$. This is called deep depletion condition of the MOS capacitor and it's a large signal regime. If we apply on this step increase a δV_g this will modulate the width of the depletion layer (in low and high frequency too) because we don't have electron at the interface. The capacitance is $C_s = C_{dep} = \epsilon_{si}/W_d$ so the total capacitance will decrease over V . W_d is related to V_s so $W_d > W_d^{max}$ means $V_s > 2|\phi_b|$ the conduction band can bend even below the Fermi level but we have to keep the condition of no electrons at the interface so we have the split in the two Fermi level for electrons and holes. Small voltage drop over the oxide due to big voltage drop over the substrate. GR processes will pull the system to the LF regime in order to restore the equilibrium so with a Q_{inv} of

electrons at the surface.



Let's

study the behaviour in time of this charge under the simplifying assumption that Q_s remains constant: so by S-R-H statistic

$$\frac{dQ_{inv}}{dt} = -qG[W_d(t) - W_d^{max}] = -q\frac{n_i}{2\tau_0}[W_d(t) - W_d^{max}] \quad (4.35)$$

but $Q_s = Q_{inv} + Q_{dep} = Q_{inv} - qN_a W_d(t)$

from here we get that $W_d(t) = (Q_{inv} - Q_s)/(qN_a)$ where

Q_s is a constant so we get the following differential equation

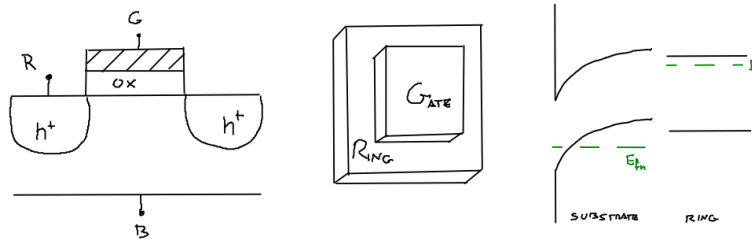
$$\frac{dQ_{inv}}{dt} = \frac{n_i}{2\tau_0 N_a} Q_{inv} + \frac{qn_i}{2\tau_0} \left[\frac{Q_s}{qN_a} + W_d^{max} \right] \quad (4.36)$$

that is a simple first order differential equation which solution is

$$Q_{inv}(t) = [Q_s + qN_a W_d^{max}][1 - e^{-t/t_g}] \quad t_g = \frac{2\tau_0 N_a}{n_i} \quad (4.37)$$

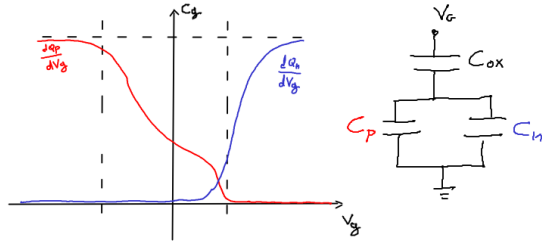
so an exponential increase of the charge with a time constant t_g

4.5 MOS capacitor with ring



We want to modify the structure adding a contact that can provide a lot of electrons. This contact is called ring it's n^+ doped. With $V_g > V_t$ E_{fn} goes down but the Fermi level in the ring is higher than it so there is a flow of electrons from the ring to the substrate with a time constant similar to the transient time from the 2 zones of the electrons.

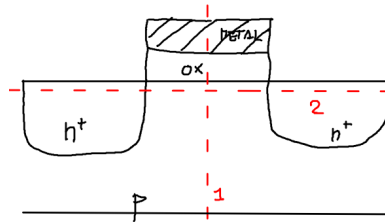
4.5.1 Split C-V curve



With this structure it's possible to measure the current of electrons and holes independently and split the 2 contributions. Let's assume that in accumulation regime and weak inversion we modulate only dQ_p (no dQ_n flow) so the capacitance is only $\frac{dQ_p}{dV_g} = C_g$ because $\frac{dQ_n}{dV_g} = 0$. At strong inversion we modulate only electrons because we reach the maximum width of the depletion layer so $\frac{dQ_p}{dV_g} = 0$ and $\frac{dQ_n}{dV_g} = C_g$. In this way we are splitting the total gate

capacitance in 2 contributions due to holes and electrons.

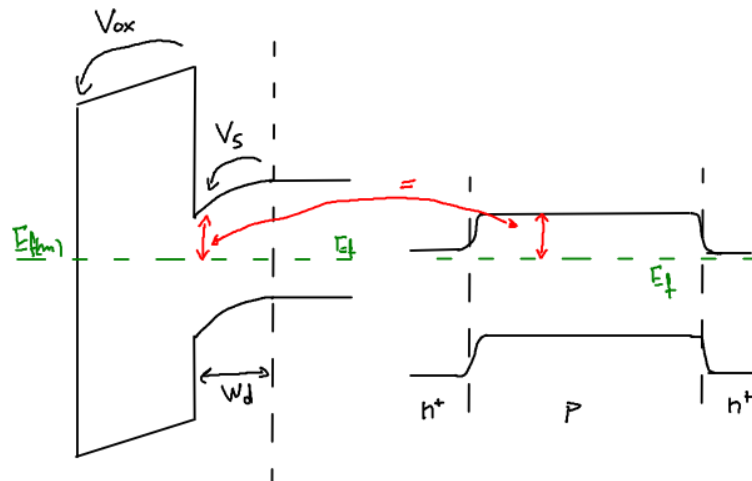
4.5.2 Electrostatic



Because the MOS capacitor is an intrinsic 2D device we have to study the electrostatics in the 2 directions of the graph.

We are not interested in polarization with $V_r < 0$ because this will make the pn junction in forward bias.

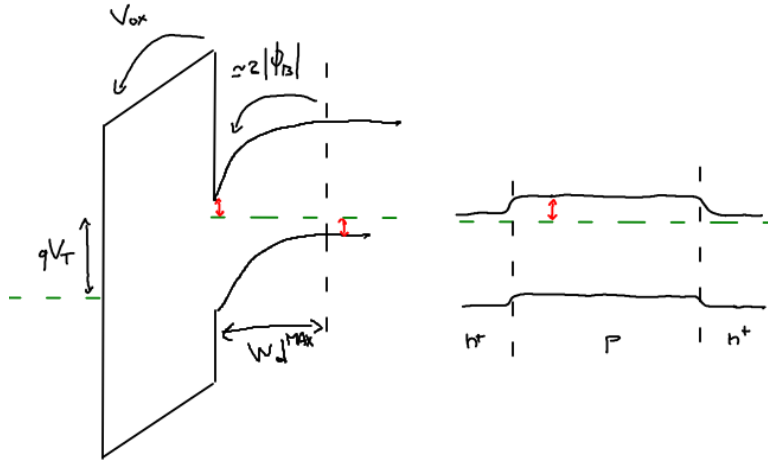
$$\rightarrow V_r = V_g = 0$$



We are under th.eq we are not perturbing the device. In cross-section 1 we have weak inversion. In cross-section 2 we have 1 single Fermi level for th.eq from cross-section 1 we know the distance

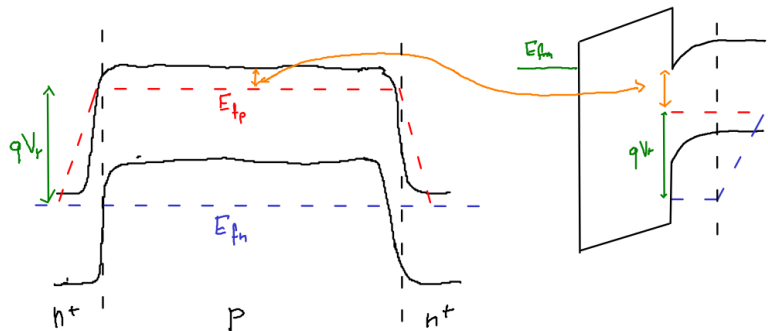
between the conduction band and E_f in the substrate. The region under the gate in graph 2 is depleted

$$\rightarrow V_r = 0 \quad V_g = V_t$$



First graph is the one we have already seen. In crosssection 2 we make the same consideration as before.

$$\rightarrow V_r > 0 \quad V_g = 0$$



We have no change in the vertical crosssection wrt the first case. For the horizontal crosssection we have to set the distance $E_c - E_f$ under the gate in accord to the first graph. In the n^+ region we are applying a potential that bands the band downwards by an amount qV_r giving a large band bending and so a separation of the Fermi levels.

The quasi Fermi level for electrons has to stay constant for simmetry E_{fp} changes.

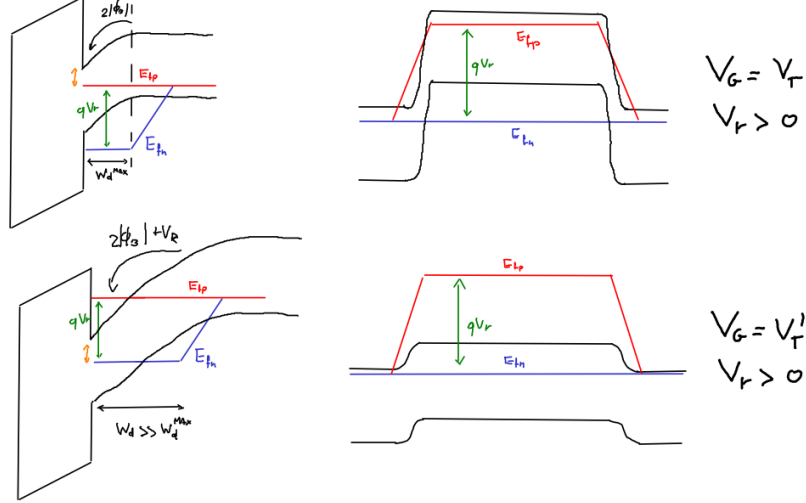
Form this we have to modify graph 1 where E_{fn} is moved downwards by an amount qV_r (doing this we do not change the electrostatic beacuse the electron concetration was already negligible so no other modifications in the band bending are needed).

$$\rightarrow V_r > 0 \quad V_g = V_t$$

Crossection 1 same as the case of $V_r = 0 \quad V_g = V_t$ with the same step of before we get the separation of the quasi Fermi levels in the first graph and the same graph for crossection 2 of

the previous case.

In this case we are no more in strong inversion due to the shift downwards of E_{fn} of qV_r . To gain the strong inversion regime we have to apply a stronger gate bias $V_g = V_t'$ to have $V_s = 2|\phi_b| + V_r$ and of course a wider depletion layer.

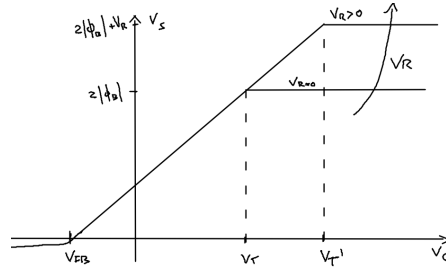


We prolong the depletion regime applying $V_r > 0$ changing the on-set of the strong inversion regime to

$$V_t' = V_{fb} + 2|\phi_b| + V_r + \frac{\sqrt{2\varepsilon_{si}qN_a(2|\phi_b| + V_r)}}{C_{ox}} \quad (4.38)$$

adding and removing $\frac{\sqrt{2\varepsilon_{si}qN_a2|\phi_b|}}{C_{ox}}$ we obtain

$$V_t' = V_t(V_r = 0) + V_r + \frac{\sqrt{2\varepsilon_{si}qN_a}}{C_{ox}} [\sqrt{2|\phi_b| + V_r} - \sqrt{2|\phi_b|}] \quad (4.39)$$



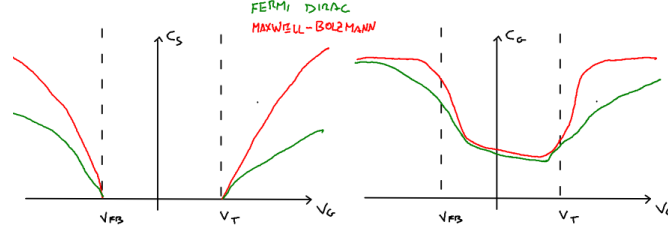
Looking at the graph of $V_s(V_g)$ we're basically making the depletion regime longer until V_t' where $V_s \simeq 2|\phi_b| + V_r$ and we gain again the strong inversion.

This is exactly the working principle of the MOS transistor; from a point on of the channel length the drop of the potential V_{ds} (that is our V_r here) is too large and strong inversion is no more possible.

The charge in the substrate will be from the relation $V_g - V_{fb} = V_s - Q_s/C_{ox}$

$$Q_{inv} = Q_s - Q_{dep}^{max} = -C_{ox}(V_g - V_{fb} - 2|\phi_b| - V_r - |Q_{dep}^{max}|/C_{ox}) = -C_{ox}(V_g - V_t') \quad (4.40)$$

In accumulation and strong inversion the MB approximation isn't valid and gives us a big error wrt the FD. Below there are the graph for the 2 distribution for $C_s - V_g$ and $C_s - V_g$.

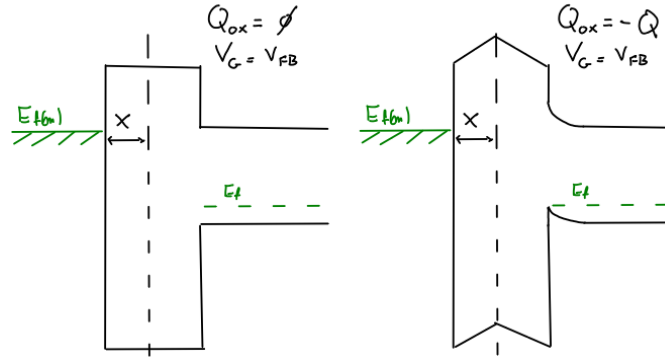


4.6 Effects of non idealities

4.6.1 Charge in the oxide

Charge in the oxide is caused due to spurious states inside the dielectric or defects that trap charges furthermore ageing increase the density of this imperfections.

Let's assume a MOS capacitor at the flat band condition with a negative charge sheet at distance x from the gate.



The negative charge decreases the potential so bands upwards the bands. We have a linear banding because the charge is concentrated in one point.

We have a layer of hole at the the substrate and also a positive charge on the gate (electrostatic induction tends to nihil the charge). The important fact is that $V_s \neq 0$ with the flat-band voltage.

To recover the flat band state we have to decrease $E_{f(m)}$ so increase the gate voltage; the new flat band voltage will be $V'_{fb} = V_{fb} + \Delta V_g$. With Gauss law we get

$$\Delta V_g = -\frac{Q_{ox}}{\epsilon_{ox}}x \quad (4.41)$$

This expression can be re-written introducing the parameter $C_{xg} = \epsilon_{ox}/x$ the capacitance between x and the gate as

$$\Delta V_g = -\frac{Q_{ox}}{C_{xg}} \quad (4.42)$$

The maximum value for this voltage variation is when $x = t_{ox} \rightarrow C_{xg} = C_{ox}$. This is reasonable result lower the distance higher the electrostatic induction.

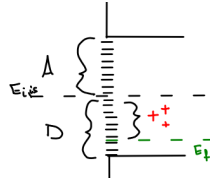
The above results are general and valid for all working regimes of the MOS capacitor.

The effect of this phenomena results in the C-V curve as a shift rightwards if the charge is negative, leftwards if the charge is positive, of ΔV_g .

If we get a distribution of charge per unit volume of ρ we get

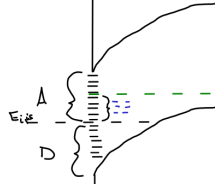
$$\Delta V_g = \int_0^{t_{ox}} \frac{x\rho}{\varepsilon_{ox}} dx \quad (4.43)$$

4.6.2 Interface states



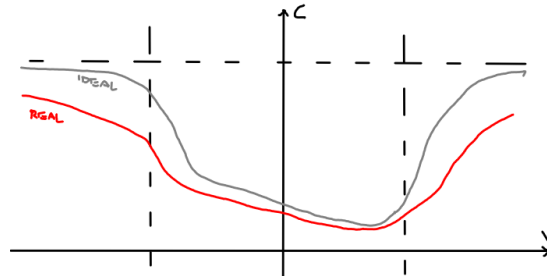
First we will consider the flat-band condition.

Acceptor states are all empty so no charge as the donor states below E_f that are all filled. There are some donor empty that gives us a positive charge (that make the potential higher and so decrease the bands). Following the results of the charge sheet in the oxide we can restore the ideal case by applying a $\Delta V_g = -Q_i/C_{ox}$.



In strong inversion we have a negative charge exposed that can be compensated with an extra voltage as before but with opposite sign.

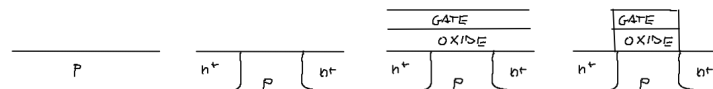
In accumulation and flat-band regime we have a negative increase so a shift leftwards of the C-V curve for the strong inversion vice versa so we have a stretch of the total C-V characteristic.



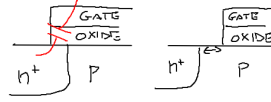
4.7 Impact of polysilicon gate

The benefit of using the polysilicon gate comes from technological issues.

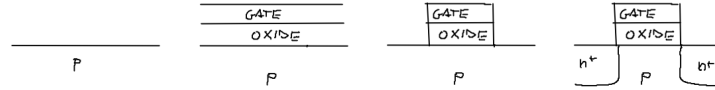
First way to do ring-MOS was by create a p-substrate, create the n^+ regions, let the oxide deposit all over, deposit the gate and then remove by etching the excess of gate and oxide. This type of process is a non self-align process.



Processes tollerances define where the gate is placed. If the gate is over the n^+ zone there will be a big parassite capacitance but on the other hand with the gate far from that zone there will be no control of electrons by the gate.



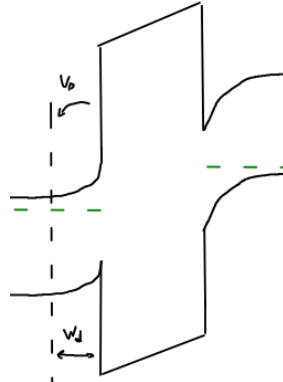
A better process is : p-substrate, deposit the oxide, deposit the gate, etching excess and than n-dope. This is a self aligned process.



To dope we have to do a heat threathment at 800C so this process does not works with metals (melting point issues) but works with polysilicon.

Also another improvmen comes from the threshold voltage $V_t = V_{fb} + 2|\phi_b| + |Q_{dep}^{max}|/C_{ox}$ that with a poly-p-doped gate is $\simeq 2|\phi_b| + |Q_{dep}^{max}|/C_{ox}$ but with a n-doped-poly is reduced to $V_t = |Q_{dep}^{max}|/C_{ox}$ beacuse $V_{fb} \simeq -1V$ in this case and $2|\phi_b| \simeq 1V$.

The problem with this gate material is that we have to consider the charge as for unit volume not as untit area (we don't have that much electrons as in a metal) so doing we get a depletion layer also in the gate of $W_d = \sqrt{\frac{2\epsilon_{si}V_p}{qN_d^g}}$ and so an additional voltage drop V_p and an additional capacitance.



The voltage ballance is now $V_g - V_{fb} = V_s + V_{ox} + V_p$ deriving wrt $-Q_s$ we get

$$\frac{1}{C_g} = \frac{1}{C_s} + \frac{1}{C_{ox}} + \frac{1}{C_g} \quad (4.44)$$

The C-V curve doesn't change until strong inversion when this phenomena becomes dominant. We can write that

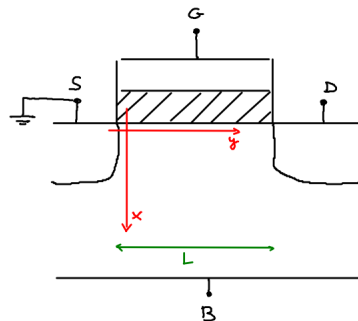
$$\frac{1}{C_g} = \frac{2kT/q}{Q_p} + \frac{1}{C_{ox}} + \frac{Q_p}{qN_d^g\epsilon_{si}} = \frac{2kT/q}{Q_p} + \frac{1}{C_{ox}} + \frac{W_d^g}{\epsilon_{si}} \quad (4.45)$$

the last term becomes dominant in strong inversion.

This is why we now use again metal for gate (with particular mix with high melting point).

Chapter 5

MOS transistor



We start our analysis of the MOS-transistor with the hypothesis of an ideal dielectric (SiO_2) and constant doping concentrations.

This is an intrinsically bi-dimensional device we will study it in the cross-section showed in figure and assuming that all is homogeneous in the orthogonal direction.

The most important region of the device is the "channel region" of length L that is the one under the gate between the 2 n-doped regions. We will consider in our analysis the two x and y axes placed as in figure.

We want to study the electrostatic of this device changing the bias of the four pins; without lack of generality since we are interested in the voltage difference we ground the source for all our analysis.

Working principles

If V_{gs} is low (until depletion regime) there is no interaction between source and drain but if we move to higher V_{gs} (inversion region) we get a lot of electrons from source to drain for the inversion layer so a flow of current it's possible under the gate. The behaviour of the device is like a resistor.

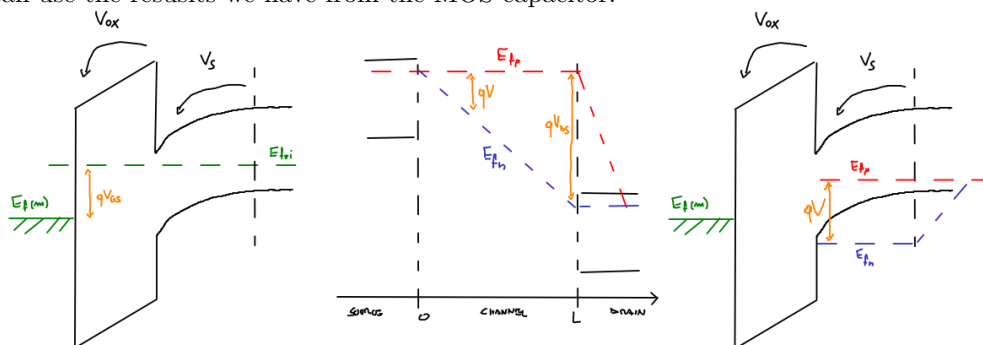
Holes have a minor role in the behaviour of the device this is why the MOS transistor (also called field effect unipolar transistor) is an unipolar device.

5.1 Gradual channel approximation

To study the electrostatic of this device we have to ideally solve the bi-dimensional Poisson equation but we can simplify our analysis studying only long channel MOS: we define a channel "long" if we can use the gradual channel approximation.

The gradual channel approximation says that the electrostatic in the channel region is a quasi 1-D electrostatic and so we can approximate every vertical crosssection as a MOS capacitor. If L is large the electric field in the y direction is very small and the dominant electric field is in the vertical direction.

We can use the results we have from the MOS capacitor.



Assuming $V_{gs} > 0$ and $V_{ds} > 0$ along the first crosssection we get what we've studied with the MOS capacitor but in the second crosssection we have a split of the 2 quasi-Fermi levels due to the shift downwards of the drain bands of an amount of qV_{ds} so the substrate is no longer at the eq. and so also the first graph have to be changed. E_{fp} remains constant over the channel but E_{fn} changes.

Placing the 0 level to E_{fp} that doesn't change we introduce the parameter

$$V = -\frac{E_{fn}(y)}{q} = V(y) \quad (5.1)$$

V goes from 0 (at the source) to V_{ds} (at the drain).

5.2 Poisson equation

Looking at the last band diagram we plotted the Poisson equation it's very similar to the one of an MOS capacitor the only difference is in the n term that now is

$$n = \frac{n_i^2}{N_a} e^{q\Delta\phi/kT} e^{-qV/kT} \quad (5.2)$$

The last exponential takes into account the decrease of the quasi-Fermi level for electrons that is far from the conduction band wrt the MOS capacitor case.

Check: if $n(0) = \frac{n_i^2}{N_a} e^{qV_s/kT} e^{-qV/kT}$ let's consider $n(0) = N_a$ (strong inversion at the source) we get $e^{-2|\phi_b|/kT} e^{-qV/kT} e^{qV_s/kT} = 1$ and so

$$-2|\phi_b| + V_s - V = 0 \quad V_s = 2|\phi_b| + V \quad (5.3)$$

Repeating all calculation done for the expression we get is similar to the one with the mos capacitor

$$\left(\frac{d\Delta\phi}{dx}\right)^2 = \frac{2kTN_a}{\varepsilon_{si}} \left[e^{-q\Delta\phi/kT} + \frac{q\Delta\phi}{kT} - 1 + \frac{n_i^2}{N_a^2} \left((e^{q\Delta\phi/kT} - 1)e^{-qV/kT} - \frac{q\Delta\phi}{kT} \right) \right] \quad (5.4)$$

we change the term that takes into account the electron concentration.

With this result we know $F_x^2 = \left(\frac{d\Delta\phi}{dx}\right)^2$ and that $F_x(x, y) = F_x(\Delta\phi, V)$.

5.3 Charge in the substrate

At the silicon surface the field is $F_s = F(0, y) = F(V_s, V)$ from this with the Gauss law we can say that the charge in the substrate (in weak and strong inversion that are the interesting regimes) is

$$Q_s \simeq -\sqrt{2\varepsilon_{si}kTN_a} \left(\frac{qV_s}{kT} + \frac{n_i^2}{N_a^2} e^{q(V_s-V)/kT} \right)^{1/2} \quad (5.5)$$

Now to divide the contribution coming from the inversion charge and from the depletion layer we have to refer to the different regimes.

5.3.1 Charge in weak inversion

In weak inversion we have that $Q_s = Q_{inv} + Q_{dep}$ using Taylor expansion of the exponential term we arrive at the following results

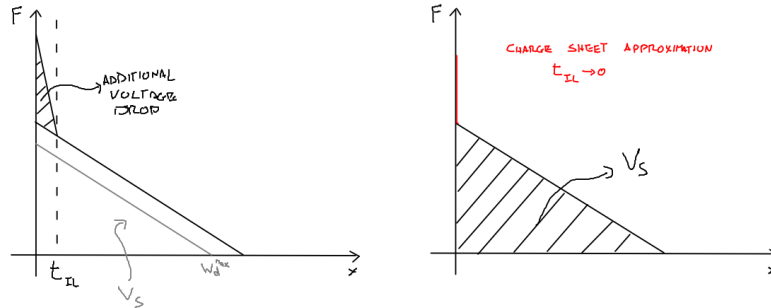
$$Q_{dep} = -\sqrt{2\varepsilon_{si}qN_aV_s} \quad Q_{inv} = -\sqrt{\frac{\varepsilon_{si}qN_a}{2V_s}} \frac{kT}{q} \frac{n_i^2}{N_a^2} e^{q(V_s-V)/kT} \quad (5.6)$$

In the y axes E_c, E_v are flat and $F_y^{weak.i} \simeq 0$ so current transport is a diffusion process and the flow of holes is negligible.

Note that since the electrons' concentration is negligible in the source, and further decreases along y, along the channel the bands are flat: as a result, the electric field is almost nil and current transport is mainly given by diffusion, not by drift.

5.3.2 Charge in strong inversion

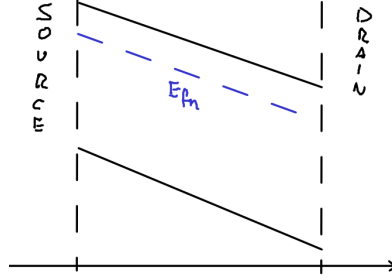
The expression seen before for the depletion charge is no longer valid in strong inversion because the concentration of electrons isn't negligible and the inversion layer charge change the F profile



To recover that expression we can make a charge sheet approximation that is considering the thickness of the inversion layer so small to be negligible to have a graph like in figure above. Making this approximation we conclude that

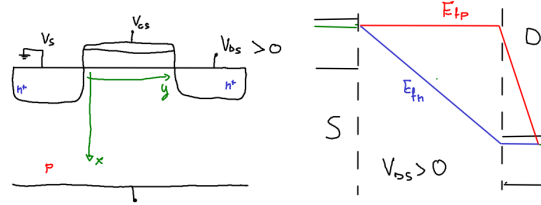
$$Q_{dep} = -\sqrt{2\epsilon_{si}qN_aV_s} \quad Q_{inv} = Q_s - \sqrt{2\epsilon_{si}qN_aV_s} \quad (5.7)$$

In strong inversion the electrons concentration is no more negligible and at the drain $E_{fn} < E_{fp}$ and bands move downwards from source to drain as the quasi-Fermi level for electrons so there will be a drift flow of electrons and a relevant electric field in the y direction.



We have at source $V_s = 2|\phi_{bi}|$ whereas at drain $V_s = 2|\phi_{bi}| + V_{DS}$: this means that the bands must move downwards along the channel, where therefore we highlight the presence of a field, creating this time a drift current.

5.4 Current behaviour



In order to arrive to $V_s(V_{gd}, V_{ds})$ we have to use not only $V_{gs} + V_{fb} = V_s + V_{ox} = V_s - Q_s/C_{ox}$ but also the continuity equation for electrons because the substrate isn't at th.eq.

We assume the device stationary and the GR processes negligible so J_n is constant in the channel region. From the interface with the oxide to the substrate the current will decrease due to the decrease of electron concentration but from S-D J will remain constant because the direction is parallel to the current flow so we can say that

$$I_{ds} = -W \int_0^{t_{inv}} J_n(x) dx \quad (5.8)$$

where t_{inv} is the thickness of the inversion layer and we simply multiply by W because we supposed that everything is constant in that direction. The minus sign is because we want positive the current that enter in the drain.

So taking into account drift and diffusion process we have

$$I_{ds} = W \int_0^{t_{inv}} n \mu_n \frac{dE_{fn}}{dx} dx \quad (5.9)$$

we know that $\frac{dE_{fn}}{dx} = -q\frac{dV}{dy}$ so solving the integral we get

$$I_{ds} = -\mu_n W \frac{dV}{dy} Q_{inv} \quad (5.10)$$

This is the differential form of the drain current in MOS transistor and making another step of integration we come to

$$I_{ds} = -\mu_n \frac{W}{L} \int_0^{V_{ds}} Q_{inv} dV \quad (5.11)$$

the integral form for drain current. This expressions (differential and interal) are general.

Let's now focus on strong inversion regime.

In this regime we've seen that using the charge sheet approximation $Q_{inv} = Q_s + \sqrt{2\varepsilon_{si}qN_aV_s}$ if we combine this equation with

$$Q_s = -\sqrt{2\varepsilon_{si}kTN_a} \left(\frac{qV_s}{kT} + \frac{n_i^2}{N_a^2} e^{q(V_s-V)/kT} \right)^{1/2} \quad (5.12)$$

and with $V_{gs} + V_{fb} = V_s - Q_s/C_{ox}$ we get that $V_s \simeq 2|\phi_b| + V$ and $Q_s = -C_{ox}(V_{gs} - V_{fb} - V_s)$ if we use this two equation with the first one (inversion charge) we get that

$$Q_{inv} \simeq -C_{ox}(V_{gs} - V_{fb} - 2|\phi_b| - V) + \sqrt{2\varepsilon_{si}qN_a(2|\phi_b| + V)} \quad (5.13)$$

we will not solve this equation but we will consider some different regimes

5.4.1 Ohmic regime $V_{ds} \ll 2|\phi_b|$

If V_{ds} is small also V will be small so we can neglect that contribution

$$Q_{inv} \simeq -C_{ox}(V_{gs} - V_{fb} - 2|\phi_b| - \frac{Q_{dep}^{max}}{C_{ox}}) \simeq -C_{ox}(V_{gs} - V_t) \quad (5.14)$$

so putting this result in the integral form for the current and solving the integral we get

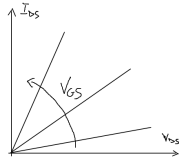
$$I_{ds} = \mu_n C_{ox} \frac{W}{L} (V_{gs} - V_t) V_{ds} \quad (5.15)$$

This is the expression for ohmic regime the current is proportional to V_{ds} .

The inversion charge does not change from source to drain and because V_{ds} is very small the electrostatic is almost uniform along the channel.

It's like having a resistor in the channel

that can be modulate by V_{gs} . We can define a resistivity for the channel as



$$R_{ch} = (\frac{\partial I_{ds}}{\partial V_{ds}})^{-1} = \frac{1}{\mu_n C_{ox}(V_{gs} - V_t)} \frac{L}{W} = \rho_{sh}^ch \frac{L}{W} \quad (5.16)$$

We expect the field constant and so equal to V_{ds}/L .

5.4.2 Parabolic regime $V_{ds} < 2|\phi_b|$

Now V_{ds} is no more negligible but enough small to make a Taylor expansion of the second terms as

$$Q_{inv} \simeq -C_{ox}(V_{gs} - V_{fb} - 2|\phi_b| - V) + \sqrt{2\varepsilon_{si}qN_a 2|\phi_b|} \left(1 + \frac{1}{2} \frac{V}{2|\phi_b|}\right) = -[...] + \sqrt{\frac{\varepsilon_{si}qN_a}{4|\phi_b|}} V = -[...] + |Q_{dep}^{max}| + C_{dep}V \quad (5.17)$$

and so re-writing the equation

$$Q_{inv} \simeq -C_{ox}(V_{gs} - V_{fb} - 2|\phi_b| - \frac{Q_{dep}^{max}}{C_{ox}} - V(1 + \frac{C_{dep}}{C_{ox}})) = -C_{ox}(V_{gs} - V_t - mV) \quad (5.18)$$

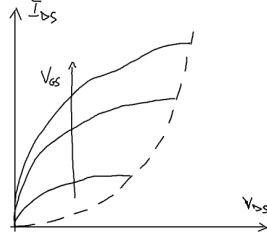
The term $-mV$ is an increase of the threshold voltage from source to drain.

" $-mV$ " is an increase of the threshold voltage from source to drain like in the case of MOS-capacitor with ring. We have V_t at source but at drain $V_t' = V_t + mV$ recovering the expression for the charge from MOS-capacitor with ring $Q_{inv} = -C_{ox}(V_{gs} - V_t')$

The inversion charge is decreasing from source to drain; putting this equation in the integral we get

$$I_{ds} = \mu_n C_{ox} \frac{W}{L} [(V_{gs} - V_t)V_{ds} - \frac{mV_{ds}^2}{2}] \quad (5.19)$$

we have a parabolic behaviour of the current. If V_{ds} is small we can neglect the quadratic term and so recovering the previous condition.



The current deviates from the linear behavior, increasing less than linearly and reaching an horizontal tangent point: this is due to V_{DS} being large, which determines a non negligible reduction of the inversion charge, which triggers an increase of the electric field to maintain the current constant; however, since the charge is decreasing, we are increasing the channel resistance, which is not constant anymore.

5.4.3 Saturation point

We can call the current and voltage of the vertex of the parabola saturation's one

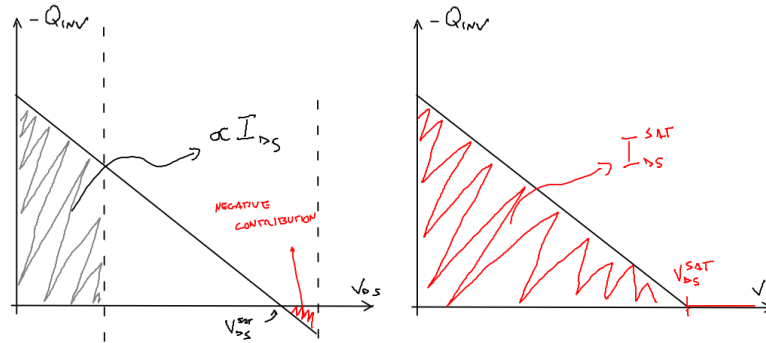
$$V_{ds}^{sat} = \frac{V_{gs} - V_t}{m} \quad I_{ds}^{sat} = \mu_n C_{ox} \frac{W}{L} \frac{(V_{gs} - V_t)^2}{m} = \mu_n C_{ox} \frac{W}{L} \frac{(V_{ds}^{sat})^2}{m} \quad (5.20)$$

Increasing V_{ds} we increase the electric field and decrease the charge (so we get a more resistive channel). At V_{ds}^{sat} the charge at the drain is

$$Q_{inv}(y = L) = -C_{ox}(V_{gs} - V_t - m \frac{V_{gs} - V_t}{m}) = 0 \quad (5.21)$$

this is called the pinch off condition of the transistor. If from the saturation point on we keep using the previous equation we get a reduction of the current that has no sense.

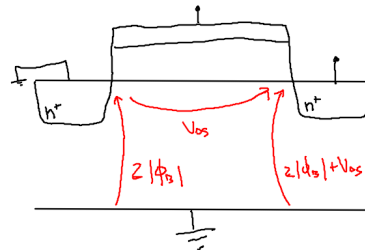
Mathematical explanation of dicendent parabola



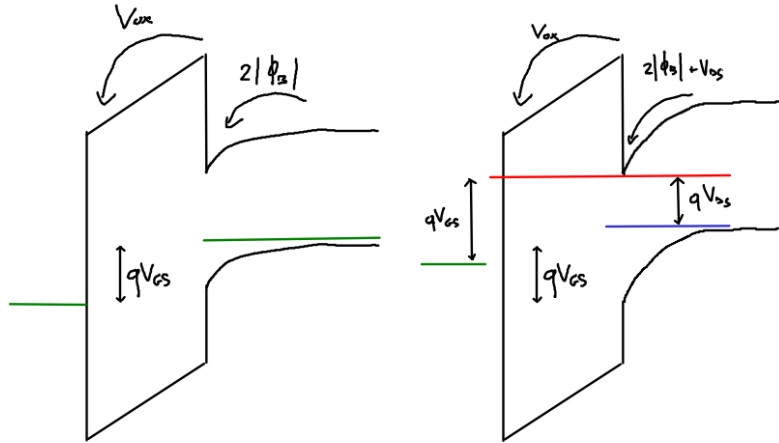
Let's consider $-Q_{inv}(V_{ds})$ we calculated the area of this expression to find the current so the area under the rect in the graph is proportional to the current. When $V_{ds} = V_{ds}^{sat}$ we are at the vertex of the parabola and so the current is proportional to the area of the triangle.

From there on we add negative area contribution that has no sense it's like accumulating holes in the inversion layer. At the drain we were at the limit of strong inversion regime if we increase V_{ds} over the saturation point we enter at the drain at weak inversion regime where electrons concentration can be apporoximated as negligible. The real graph of the inversion charge becomes zero over the saturation voltage so from the vertex on the current remains constant.

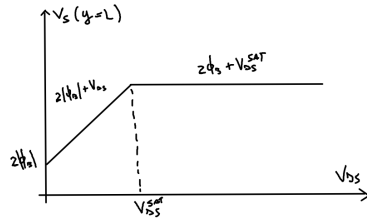
Physical explanation of dicendent parabola



Start from the condition of V_{gs} big enough to have strong inversion in the channel; at source we will have a single Fermi level at drain 2 Fermi levels displaced by qV_{ds} . Since we are keeping strong inversion the bands must move down to keep E_{fn} close to E_c .



Let's look at $V_s(y=L)$ at the drain side as V_{ds} increases; if V_{ds} is small $V_s \simeq 2|\phi_b|$ and increasing the drain voltage we will increase also $V_s \simeq 2|\phi_b| + V_{ds}$. When V_{ds}^{sat} is reached what happen.



We consider the $V_s - V_{ds}$ plot at constant V_{gs} by increasing V_{ds} we have V_s closer to the V_t' (threshold voltage also at the drain) and the onset of weak inversion. When we reach the intersection V_s does not change any longer and the drain loses control of the electrostatics; the channel and the electric fields in the y direction does not change anymore so we reach the maximum band bending.

$Q_{inv} = 0$ does not mean really zero but negligible electron concentration (we are in weak inversion).

The parameter $m = 1 + \frac{C_{dep}}{C_{ox}}$ involves doping concentration and oxide thickness and express how much of V_g drops over the substrate; for a good mos $m=1,1-1,4$.

We now want to give a more physically detailed description of the saturation condition. We are stating that V_{GS} is large enough to provide strong inversion regime in the channel: at source we will have one single Fermi level, whereas at drain we will have two Fermi levels displaced by qV_{DS} ; since we are keeping strong inversion, the bands must move down too, so to keep E_{Fn} close to E_C .

Let's now look at $V_s(y = L)$, so at the drain side, as V_{DS} increases: if V_{DS} is small, $V_s = 2|\phi_B|$; increasing V_{DS} , V_s increases proportionally as $V_s = 2|\phi_B| + V_{DS}$; when V_{DS}^{sat} is reached, we must study deeper to understand V_s 's behavior.

We consider the $V_s - V_G$ plot: given a constant V_{GS} , by increasing V_{DS} we move V_s closer to V_t' (the electrostatic threshold voltage at drain) at the onset of weak inversion. When a crossing is reached, V_s does not change any longer, because the intersection no longer changes. As a result, V_s does not change anymore and the drain loses control of the electrostatics of the channel: the fields in the y-direction do not change any longer, thus the bands' bending reaches its maximum value. Notice that stating $Q'_{inv} = 0$ at the drain means that the charge becomes negligible for the electrostatics (charge can never be actually null).

5.5 Over the saturation point

We still don't know E_{fn} along the channel or the voltage drop in function of y.

From the differential form of the drain current we have $I_{ds} = -\mu_n W \frac{dV}{dy} Q_{inv}$ we can integrate this expression up to a potential V in a point y

$$\int_0^y I_{ds} dy = \int_0^V -\mu_n W Q_{inv} dV \quad (5.22)$$

$$I_{ds} y = \int_0^V \mu_n W C_{ox} (V_{gs} - V_t - mV) dV = \mu_n W C_{ox} [(V_{gs} - V_t)V - \frac{mV^2}{2}] \quad (5.23)$$

but we know from the parabolic regime another expression for

$I_{ds} = \mu_n \frac{W}{L} C_{ox} [(V_{gs} - V_t)V_{ds} - \frac{mV_{ds}^2}{2}]$ so we can get V(y) as

$$V(y) = \frac{V_{gs} - V_t}{m} - \sqrt{\left(\frac{V_{gs} - V_t}{m}\right)^2 - \frac{2y}{L} \left(\frac{V_{gs} - V_t}{m}\right) V_{ds} + \frac{y}{L} V_{ds}^2} \quad (5.24)$$

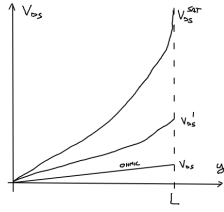
from that we know E_{fn} because $V = -E_{fn}/q$.

This result is general but we will study it in the various regime; in ohmic region V_{ds} is small so we can neglect the quadratic term and extract the $\frac{V_{gs}-V_t}{m}$ term from the square root, in this way making a Taylor expansion we get

$$V(y) \simeq \frac{V_{gs} - V_t}{m} - \frac{V_{gs} - V_t}{m} \sqrt{1 - \frac{2y}{L} V_{ds} / \left(\frac{V_{gs} - V_t}{m}\right)} \simeq \frac{V_{gs} - V_t}{m} - \frac{V_{gs} - V_t}{m} \left(1 - \frac{y}{L} V_{ds} / \left(\frac{V_{gs} - V_t}{m}\right)\right) \quad (5.25)$$

$$V \simeq \frac{V_{ds}}{L} y \quad (5.26)$$

reasonable result when the channel is uniform and we said that $\frac{dV}{dy}$ has to be constant so V linear function of y. We get a constant drift contribution over the channel.

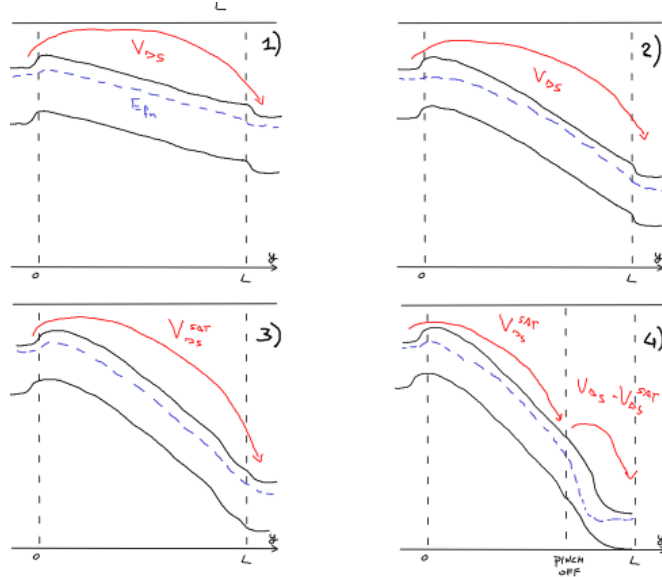


Increasing the drain voltage we enter in the parabolic regime and the charge will decrease and, because the differential form of the current must be always valid, $\frac{dV}{dy}$ must increase (we need higher electric field). We increase the slope of the rect form source to drain.

At pinch off

point we have no charge in L so at V_{ds}^{sat} we reach L with vertical tangent. This condition means infinite electric field in y direction so F_y is no more negligible and the gradual channel approximation is no longer valid.

We have to study the 2D Poisson equation. We will not study it mathematically but let's see the results.



In ohmic regime V_{ds} is small so we get the 1) graph.

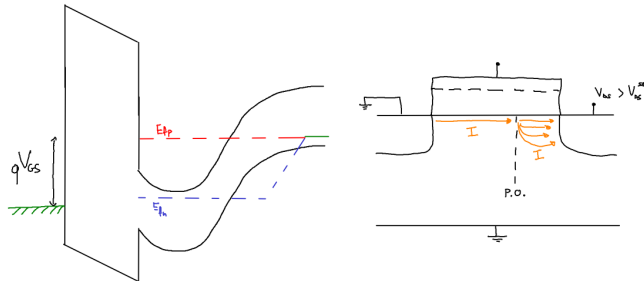
Increasing V_{ds} we increase the slope of E_{fn} that change like figure 2).

We reach the pinch off point large F very large tangent at L but not infinite like in figure 3).

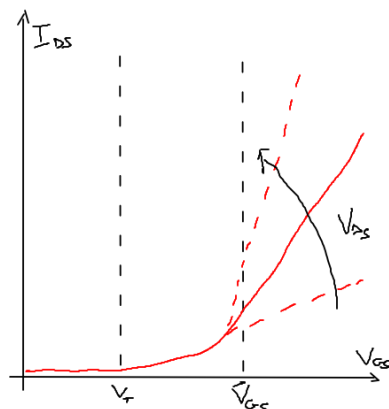
Using gradual channel approximation we said that the drain over the saturation voltage loses control of the band bending this is unreasonable; in reality the pinch off point moves leftwards for voltages higher than saturation at drain leaving a potential V_{ds}^{sat} from source to pinch-off and from pinch-off to drain $V_{ds} - V_{ds}^{sat}$. like in figure 4). This effect acts like a reduction of the L of the channel.

In the x axis the band diagram is purely 2D band-diagram; the maximum electron concentration is no more at the interface but it's spread in the vertical direction.

Beyond the pinch-off we have a depleted region.



5.6 Linear transcharacteristic



We assume V_{ds} set and we change V_{gs} and we want to know the current profile.

First region we get $V_{gs} < V_t$ so we are in accumulation or weak inversion region so the current is negligible.

When we reach $V_{gs} = V_t$ we enter in the on-state regime we are at saturation because we have V_t at the source but going to the drain the threshold voltage increase so we don't have threshold there. $I_{ds}^{sat} = \mu_n C_{ox} \frac{W}{L} \frac{(V_{gs} - V_t)^2}{2m}$ so we have a parabolic dependence.

We increase V_{gs} until we reach the threshold condition also at the drain at the voltage

$V_t' = V_t + mV_{ds} = \overline{V_{gs}}$ in this case the current is $I_{ds} = \mu_n C_{ox} \frac{W}{L} [(V_{gs} - V_t)V_{ds} - \frac{mV_{ds}^2}{2}]$ so a linear dependence.

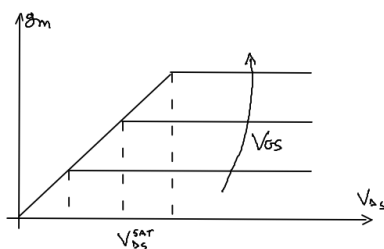
5.7 Small signal parameters

5.7.1 Transconductance g_m

If we slightly move V_{gs} we change the current flow so we can define a small signal

transconductance as $g_m = \left(\frac{\partial I_{ds}}{\partial V_{gs}} \right)_{V_{ds}}$ that in ohmic-parabolic and saturation regime is

$$g_m^{ohmic} = \mu_n C_{ox} \frac{W}{L} V_{ds} \quad g_m^{sat} = \mu_n C_{ox} \frac{W}{L} \frac{V_{gs} - V_t}{m} \quad (5.27)$$



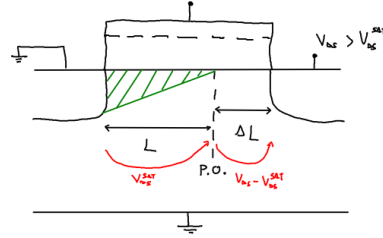
5.7.2 Transconductance g_d

We can define also $g_d = \left(\frac{\partial I_{ds}}{\partial V_{ds}} \right)_{V_{gs}}$ that for ohmic and parabolic regime is

$$g_d^{ohmic} = \mu_n C_{ox} \frac{W}{L} [(V_{gs} - V_t) - mV_{ds}] \quad g_d^{sat} = 0 \quad (5.28)$$

This last result is obviously an approximation because we implicitly used the gradual channel approximation that is not valid in saturation regime.

Using 2D Poisson equation we get that the pinch-off point moves from drain to source if $V_{ds} > V_{ds}^{sat}$; this phenomena is equivalent to a reduction of the L of the transistor that means an increase of current.



For the sake of simplicity we suppose $\Delta L \propto V_{ds}$ with direct proportionality so

$$\Delta L = \frac{V_{ds} - V_{ds}^{sat}}{F_p} \quad (5.29)$$

where F_p is the average field in the ΔL region. Moving to larger V_{ds} than V_{ds}^{sat} we can write

$$I_{ds} = I_{ds}^{sat} \frac{L}{L - \Delta L} = I_{ds}^{sat} \frac{1}{1 - \frac{\Delta L}{L}} \quad (5.30)$$

referring to a long channel device ΔL is very small compared to L so we can make a Taylor expansion obtaining

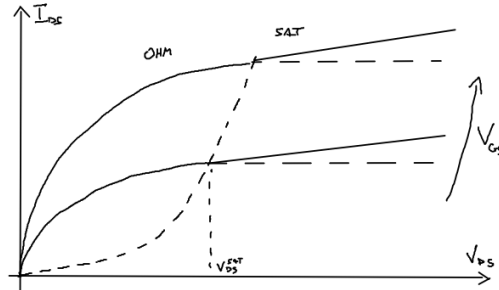
$$I_{ds} = I_{ds}^{sat} \left(1 + \frac{\Delta L}{L} \right) = I_{ds}^{sat} \left(1 + \frac{V_{ds} - V_{ds}^{sat}}{LF_p} \right) \quad (5.31)$$

we get a linear increase of the current increasing V_{ds} and also a larger slope of the rect with higher currents.

So the real output resistance is

$$g_d = \left(\frac{\partial I_{ds}}{\partial V_{ds}} \right)_{V_{gs}}^{-1} = \frac{LF_p}{I_{ds}^{sat}} \quad (5.32)$$

that is a strong function of L .



5.7.3 Capacitive terms

In this section we will introduce only intrinsic capacitive terms. We define Q_c total charge in the inversion layer as

$$Q_c = W \int_0^L Q_{inv} dy = [C] \quad (5.33)$$

if we change the integration variable by multipling and dividing by dV we get

$$Q_c = W \int_0^{V_{ds}} Q_{inv} dV \frac{dy}{dV} \quad (5.34)$$

from the differential form of the drain current we know that $I_{ds} = -\mu_n W \frac{dV}{dy} Q_{inv}$ so using this expression to derive $\frac{dV}{dy}$ we get

$$Q_c = -\mu_n \frac{W^2}{I_{ds}} \int_0^{V_{ds}} C_{ox}^2 (V_{gs} - V_t - mV)^2 dV \quad (5.35)$$

solving the integral and unsing the expression for the current we get the final result

$$Q_c = -WLC'_{ox} \frac{2}{3} \frac{m^2 V_{ds}^2 + 3(V_{gs} - V_t)^2 - 3mV_{ds}(V_{gs} - V_t)}{2(V_{gs} - V_t) - mV_{ds}} \quad (5.36)$$

This formula is general and valid for all on-state regimes but we can apporximate it for the ohmic regime when $V_{ds} \simeq 0$ and for the saturation regime where $V_{ds}^{sat} = (V_{gs} - V_t)/m$ obtaining

$$Q_c = -WLC_{ox}(V_{gs} - V_t) \quad [ohmic] \quad (5.37)$$

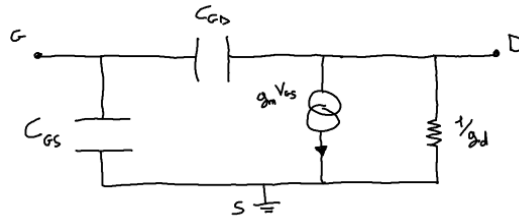
$$Q_c = \frac{2}{3} Q_c^{ohmic} \quad [saturation] \quad (5.38)$$

With this two expressions we can derive the gate and the drain capacitance as

$$C_g = -\frac{\partial Q_c}{\partial V_{gs}}|_{V_{ds}} = WLC_{ox} \left[1 - \frac{m^2 V_{ds}^2}{3(2(V_{gs} - V_t) - mV_{ds})^2} \right] \quad (5.39)$$

$$C_d = \frac{\partial Q_c}{\partial V_{ds}}|_{V_{gs}} = 2/3 WLC_{ox} \left[1 - \frac{(V_{gs} - V_t)^2}{[2(V_{gs} - V_t) - mV_{ds}]^2} \right] \quad (5.40)$$

With this parameter we can complete the small signal model of the MOS transistor



We have only to link the values C_g, C_d to the capacitance C_{gd}, C_{gs} we can do this considering a modulation of the drain/source with the other terminals grounded and probe what impedance we see; doing this procedure we get

$$C_g = C_{gs} + C_{gd} \quad C_d = C_{gd} \quad (5.41)$$

In ohmic regime we get that $C_{gs} = C_{gd} = 1/2 WLC_{ox}$ while in saturation regime $C_d = C_{gd} \simeq 0$, $C_{gs} = 2/3 WLC_{ox}$; the physical reason of this is that the drain loses control of the inversion charge only source provides electrons at the channel.

5.7.4 Frequency response

The frequency response is related to the transit time of the electrons in the channel so we can define it as

$$\tau_t = \int_0^L \frac{dy}{v_d} \quad (5.42)$$

recovering the definition used for the narrow base diode we get $\tau_t = Q_c/I_{ds}$; because Q_c isn't a linear function of I_{ds} we can only use a small signal model so

$$\tau_t = -\frac{\partial Q_c}{\partial I_{ds}} = -\frac{\partial Q_c}{\partial V_{gs}} \frac{\partial V_{gs}}{\partial I_{ds}} = C_g \frac{1}{g_m} \quad (5.43)$$

So in ohmic and saturation regimes we get

$$\tau_{ohm} = \frac{L^2}{\mu_n V_{ds}} \quad \tau_{sat} = \frac{2}{3} \frac{L^2}{\mu_n V_{ds}} \quad (5.44)$$

Smaller L we get smaller distance and greater electric field so greater velocity (over a smaller space).

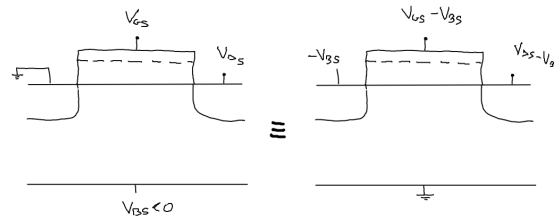
Using the cutting frequency of the transistor we find that

$$f_t = \frac{g_m}{2\pi(C_{gs} + C_{gd})} = \frac{1}{2\pi} \frac{g_m}{C_g} = \frac{1}{2\pi\tau_t} \quad (5.45)$$

Reducing L we improve frequency response, increase current and reduce intrinsic capacitances, all good effects but if we keep reducing it we lose the long channel approximation and something bad happens.

5.8 Body effect

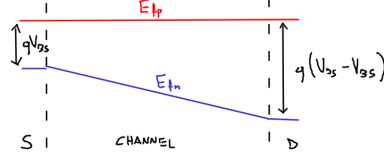
Until now we've always considered the bulk grounded now we consider the situation if we apply a $V_{bs} < 0$ (with a positive voltage we will have the 2 junction forward biased). Total voltage under the channel is now $V_{gs} - V_{bs}$. We can restore the initial condition of substrate grounded if we add at all the other pins a voltage of $-V_{bs}$ like in figure



In this case we get that $V_{gs} - V_{bs} - V_{fb} = V_s - Q_s/C_{ox}$ from this we get that the inversion charge is (under charge sheet approximation)

$$Q_{inv} = Q_s - Q_{dep} = -C_{ox}(V_{gs} - V_{bs} - V_{fb} - V_s) + \sqrt{2\epsilon_{si}qN_aV_s} \quad (5.46)$$

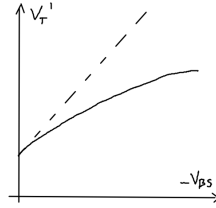
In ohmic regime $V_s \simeq 2|\phi_b| - V_{bs}$ so we get a change of the band diagram where also at the source E_{fn} is under E_{fp}



making a little bit of calculation we get that in ohmic regime

$$Q_{inv} = -C_{ox}(V_{gs} - V_{fb} - 2|\phi_b| - \frac{\sqrt{2\varepsilon_{si}qN_a(2|\phi_b| - V_{bs})}}{C_{ox}}) = -C_{ox}(V_{gs} - V'_t) \quad (5.47)$$

V'_t is the new threshold voltage of the system and we get $I_{ds} = \mu_n C_{ox} \frac{W}{L} (V_{gs} - V'_t) V_{ds}$ this expression is equal to the one with the bulk grounded but with another V'_t . For the other regimes we get the same results of bulk grounded with V'_t and for the parabolic regime m is modified.

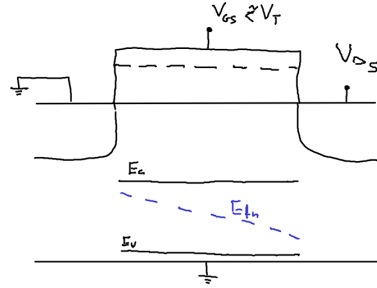


For better understand the behaviour of $V'_t(-V_{bs})$ we can study

$$\frac{dV'_t}{dV_{bs}}|_{V_{bs}=0} = \left[\frac{\sqrt{2\varepsilon_{si}qN_a}}{C_{ox}} \frac{1}{2} \frac{1}{\sqrt{2|\phi_b| - V_{bs}}} \right]_{V_{bs}=0} = \frac{C_{dep}}{C_{ox}} = m - 1 \quad (5.48)$$

5.9 Subthreshold regime

5.9.1 Current expression



In this regime $V_{gs} \lesssim V_t$ so we don't have strong inversion anywhere in the channel, the electron concentration is negligible for electrostatics that is dominated by the depletion charge. Bands are almost flat in the channel (also if electron concentration change because it's a negligible contribution).

We get a diffusion current of electrons the drift flow is negligible. Solving the poisson equation we got that $Q_{inv} = -\sqrt{\frac{\varepsilon_{si}qN_a}{2V_s}} \frac{kT}{q} \frac{n_i^2}{N_a^2} e^{q(V_s - V)/kT}$ we can use this expression to derive the current in this regime so

$$I_{ds} = -\mu_n \frac{W}{L} \int_0^{V_{ds}} -\sqrt{\frac{\varepsilon_{si}qN_a}{2V_s}} \frac{kT}{q} \frac{n_i^2}{N_a^2} e^{q(V_s - V)/kT} dV \quad (5.49)$$

We can extract from the integral the square root and V_s because they are not function of y of V so

$$I_{ds} = \mu_n \frac{W}{L} \sqrt{\frac{\varepsilon_{si} q N_a}{2V_s} \frac{kT}{q}} \frac{n_i^2}{N_a^2} e^{qV_s/kT} \int_0^{V_{ds}} e^{-qV/kT} dV \quad (5.50)$$

Solving the integral we get the following expression

$$I_{ds} = \mu_n \frac{W}{L} \sqrt{\frac{\varepsilon_{si} q N_a}{2V_s} \left(\frac{kT}{q}\right)^2} \frac{n_i^2}{N_a^2} e^{qV_s/kT} \left(1 - e^{-qV_{ds}/kT}\right) \quad (5.51)$$

we want a dependance on V_{gs} not on V_s .

As done for the MOS capacitor we use $V_{gs} + V_{fb} = V_s + \sqrt{2\varepsilon_{si} q N_a V_s} / C_{ox}$ we can assume that $V_s \lesssim 2|\phi_b|$ so we can make a Taylor expansion of $\sqrt{V_s}$ over $2|\phi_b|$ getting

$$\sqrt{V_s} \simeq \sqrt{2|\phi_b|} + \frac{1}{2} \frac{V_s - 2|\phi_b|}{\sqrt{2|\phi_b|}} \quad (5.52)$$

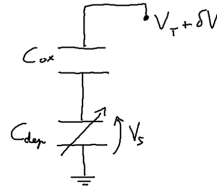
(remember $f(a) + f'(a)(x-a)$). Replacing this expression in the previous formula we get

$$V_{gs} = V_{fb} + V_s + \sqrt{2\varepsilon_{si} q N_a 2|\phi_b|} / C_{ox} + \frac{1}{2} \frac{V_s - 2|\phi_b|}{\sqrt{2|\phi_b|}} \sqrt{2\varepsilon_{si} q N_a} / C_{ox} \quad (5.53)$$

adding and removing $2|\phi_b|$ we can write that expression as

$$V_{gs} = V_t + (V_s - 2|\phi_b|)m \quad \rightarrow \quad V_s = 2|\phi_b| + \frac{V_{gs} - V_t}{m} \quad (5.54)$$

The physical meaning of this can be explained considering a system like in figure



where we can say that $V_s = 2|\phi_b| + \delta V \frac{C_{ox}}{C_{ox} + C_{dep}} = 2|\phi_b| + \frac{\delta V}{m}$.

Turning back to the expression for the current we can write it in this way now

$$I_{ds} = \mu_n C_{ox} (m - 1) \frac{W}{L} \left(\frac{kT}{q}\right)^2 e^{q(V_{gs} - V_t)/mkT} \left(1 - e^{-qV_{ds}/kT}\right) \quad (5.55)$$

That is the expression for the current in the subthreshold regime. If V_{ds} is more than a few kT the last exponential can be neglected.

The current density J_n is a pure diffusion process so we can say that $J_n = qD_n \frac{dn}{dy}$ and so

$$I_{ds} = -W \int_0^{t_{inv}} qD_n \frac{dn}{dy} dx = WD_n \frac{d}{dy} \left(\int_0^{t_{inv}} -qndx \right) = WD_n \frac{d}{dy} Q_{inv} \quad (5.56)$$

This means that Q_{inv} has to change linearly over y (stationary case without G-R so current constant over y) so that

$$I_{ds} = -WD_n \frac{Q_{inv}(0) - Q_{inv}(L)}{L} \quad (5.57)$$

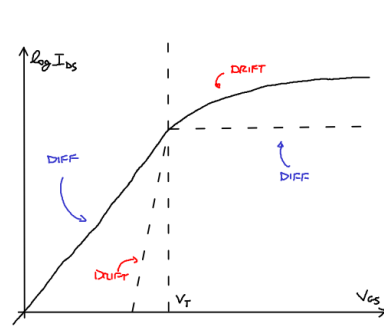
where we remember that

$$Q_{inv}(0) = \sqrt{\frac{\varepsilon_{Si} q N_a}{2 V_s}} \frac{kT}{q} \frac{n_i^2}{N_a^2} e^{q \frac{V_s}{kT}} \quad (5.58)$$

$$Q_{inv}(L) = Q_{inv}(0) e^{q \frac{V_s - V_{ds}}{kT}} \quad (5.59)$$

Since the change of charge is linear E_{fn} must drop logarithmically.

5.9.2 Transcaracteristics



Let's plot now $I_{ds}(V_{gs})$ in a logarithmic plot. We obtain for the subthreshold regime a rect with a slope defined as sub-threshold slope or STS of

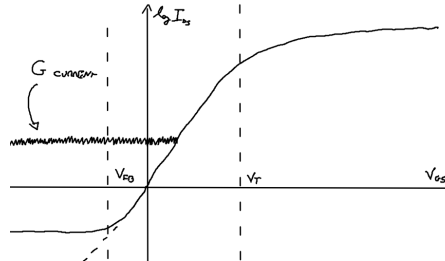
$$STS = \left(\frac{\partial \log(I_{ds})}{\partial V_{gs}} \right)^{-1} = \frac{kT}{q} \ln(10) m \quad (5.60)$$

At room temperature $STS = (60 \text{ mV/dec})m$.

Form V_t on the diffusion contribution to the current saturates and the drift becomes dominant. If we move to low current we break the assumption of flat band condition V_s becomes independent on V_{gs} (near and below the FB condition) so our expression is no more valid

and the current will saturate to a lower value.

At low current we have to take also in account the GR processes in the channel. We have a net generation process beacuse $E_{fn} < E_{fp}$ and also form the reversed bias junctions form drain-bulk. Generated electrons will assist the current flow. Typically before breaking the assumption of flat-band the current saturate due to the G process.



Improvment for MOS

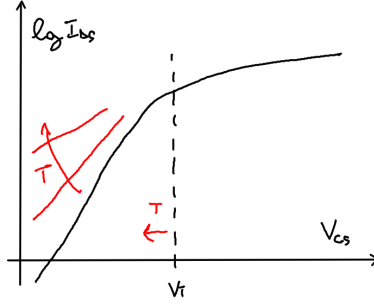
If we reduce t_{ox} the gate will have better control of the substrate and better

$$STS = \frac{kT}{q} \ln(10) (1 + (\varepsilon_{si} t_{ox}) / (\varepsilon_{ox} W_d^{max})) \text{ and also lower } V_t \propto |Q_{dep}^{max}| / (\varepsilon_{si} / t_{ox}).$$

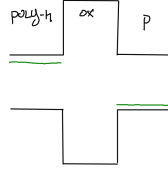
It's also good to decrease N_a to better deplete the substrate getting better STS and lower V_t

5.10 Temperature dependance

In sub-threshold regime the STS with high temperatures becomes higher and so we have a curve less steeper (rect more flat).



We have a change also of the V_t ; ϕ_b change, with T also E_f change and so the flat band voltage and also $E_{f(m)}$ change depending on what metal we are using.



Using a polysilicon gate as in figure we can say that $V_{fb} = -(\frac{E_{gap}}{2q} + |\phi_b|)$ so we can write

$$V_t = -\frac{E_{gap}}{2q} + |\phi_b| + \frac{\sqrt{2\varepsilon_{Si}qN_a2|\phi_b|}}{C_{ox}} \quad (5.61)$$

so we can study the derivative of this wrt T

$$\frac{dV_t}{dT} = -\frac{1}{2q} \frac{dE_{gap}}{dT} + \frac{d|\phi_b|}{dT} + \frac{\sqrt{2\varepsilon_{Si}qN_a2}}{C_{ox}} \frac{1}{2\sqrt{|\phi_b|}} \frac{d|\phi_b|}{dT} = -\frac{1}{2q} \frac{dE_{gap}}{dT} + \frac{d|\phi_b|}{dT} (2m-1) \quad (5.62)$$

Inside $|\phi_b| = \frac{kT}{q} \ln(N_a/n_i)$ we have temperature dependences with T and n_i so

$$\frac{d|\phi_b|}{dT} = \frac{k}{q} \ln(N_a/n_i) - \frac{kT}{q} \frac{1}{n_i} \frac{dn_i}{dT} \quad (5.63)$$

as last term we have to consider that $n_i = \sqrt{N_c N_v} e^{-E_{gap}/2kT}$ is strongly dependent on temperature so

$$\frac{dn_i}{dT} = \frac{3}{2} a T^{1/2} e^{-E_{gap}/2kT} + a T^{3/2} e^{-E_{gap}/2kT} \left(\frac{-\frac{dE_{gap}}{dT} 2kT + E_{gap} 2k}{(2kT)^2} \right) \quad (5.64)$$

Putting all this results in the first expression we get the final expression

$$\frac{dV}{dT} = -(2m-1) \frac{k}{q} \left(\ln\left(\frac{\sqrt{N_c N_v}}{N_a}\right) + \frac{3}{2} \right) + \frac{m-1}{q} \frac{dE_{gap}}{dT} \quad (5.65)$$

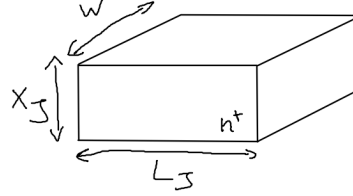
That is negative $\simeq -1mV/K$.

This phenomena have the effect to increase the offstate current.

With higher T also the mobility decrease and so the current.

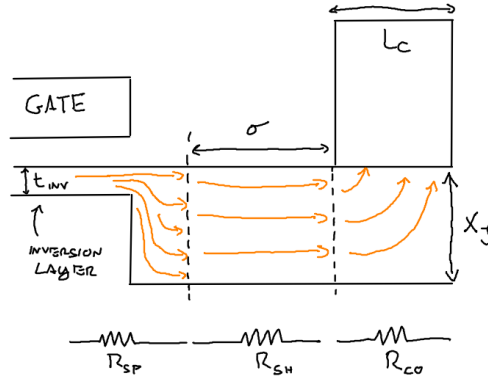
5.11 Effects of non idealities

5.11.1 Parasitic resistance of n^+ regions



Since n^+ regions are subjected to a flow of current they will show a resistance (that we suppose small since they are highly doped).

We computed the resistivity as $R = \rho_{sh} \frac{L}{W}$ putting some reasonable results we get a $\rho_{sh} = 125\Omega/sq$ that is reasonably higher than that of a metal so we have to consider it.



We have other 2 contributions over ρ_{sh} due to this parasitic resistances; vertical spreading of the electrons because they are no more subjected by an electric field and the contact resistivity. We can study this effects supposing an ideal case where we have a step-like increase in thickness from t_{inv} to X_j as in figure.

The contribution due to the vertical spread is

$$R_{sp} = \frac{2\rho_{n^+}}{\pi W} \ln(0.75 \frac{X_j}{t_{inv}}) \quad (5.66)$$

The contribution due to the finite resistance is as we said

$$R_{sh} = \rho_{sh} \frac{\sigma}{W} \quad (5.67)$$

The third contribution is

$$R_{co} = \frac{\sqrt{\rho_{sh}\rho_c}}{W} \coth(L_c \sqrt{\frac{\rho_{sh}}{\rho_c}}) \quad (5.68)$$

where $\rho_c = (\frac{\partial J}{\partial V})^{-1}$ is the contact resistivity.

This shows a different behaviour depending on L_c ; with L_c short the resistance increase in the "short contact" regime.

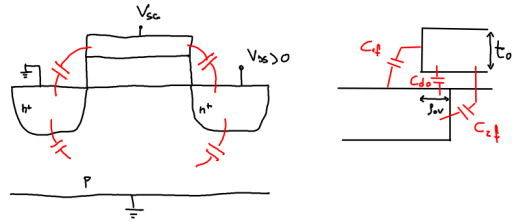
The average resistance is $R = R_{sp} + R_{sh} + R_{co} \simeq 302\Omega\mu m/W$.

This can be modeled as resistance in series with source and drain that has the effects of reducing the actual V_{ds} ; they have a relevant importance if the current is higher. If V_{gs} is increased too much the channel resistance becomes too low and the current is set by R_s R_d .

In scaling process $R_{ch} = \rho_{ch} \frac{W}{L}$ reducing L we arrive at $R_{ch} \ll R_{s,d}$ at lower gate voltages this limiting the device.

In order to avoid this problems we deposit composit material like $TiSi_2$ over the contact; this has a small resistance and already act as a contact with silicon. This treatment is also applied to the gate to avoid parasitic resistance that will decrease f response.

5.11.2 Parasitic capacitance



We can identify $n^+ - p$ junctions capacitance and gate coupling capacitance. The latter one can be divided in fringe and direct overlapped capacitance that are

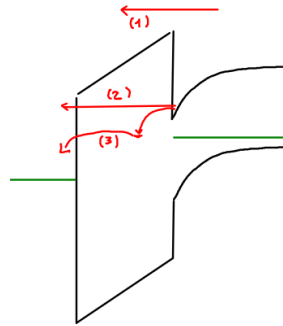
$$C_{1f} = \frac{2\varepsilon_{ox}W}{\pi} \ln\left(1 + \frac{t_g}{t_{ox}}\right) \quad (5.69)$$

$$C_{2f} = \frac{2\varepsilon_{si}W}{\pi} \ln\left(1 + \frac{X_j}{2t_{ox}}\right) \quad (5.70)$$

$$C_{do} = \frac{\varepsilon_{ox}}{t_{ox}} \rho_{ov} W \quad (5.71)$$

that are in the order of fraction of fF ($C_g \simeq 1fF$).

5.11.3 Leakage current



Considering the band diagram of a mos; electrons tend to move from substrate to the gate and they can reach this goal in three different methods. Thermionic transport is the first (1) which is difficult at room temperature due to the high barrier created by the oxide. The other 2

processes are quantum-mechanical tunneling independently (2) or with the help of a difect in the SiO_2 (3), or trap-assisted tunneling.

At RT with a low density of difect the most important contribution comes from the simple tunneling whose relevance grows as the oxide thickness is reduced.

Referring to the k space we are interested only in the right part of the parabola (electrons form Si to oxide) the current density is given by each electron ($\frac{q}{L^3}v_x(k_x)$) the barrier transparancy ($T(E_x)$) the probability of a state to be filled ($f(k_x, k_y, k_z)$) and the spin degeneracy (2) so we get

$$J_{s-ox} = \sum_{k_x > 0} 2 \frac{q}{L^3} v_x(k_x) T(E_x) f(k_x, k_y, k_z) \quad (5.72)$$

that becomes

$$J_{s-ox} = \frac{1}{(\frac{2\pi}{L})^3} \int_0^{+\infty} \int_{-\infty}^{+\infty} \int_{-\infty}^{+\infty} \frac{q}{L^3} T(E_x) v_x(k_x) f(k_x, k_y, k_z) dk_x dk_y dk_z \quad (5.73)$$

the integrals can be computed by considering $dk_{x,y,z} = \frac{m_{x,y,z}}{\hbar} dv_{x,y,z}$.

The difference wrt the metal-semiconductor junction is that here we have to use the Fermi-Dirac distribution for f beacuse we are intrested in states near E_f .

We can obtain that the current density as

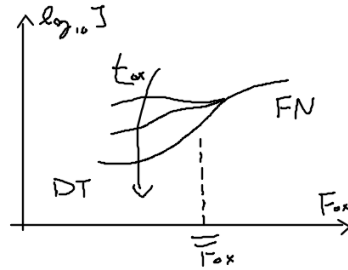
$$J = \frac{q\sqrt{m_y m_z} kT}{2\pi^2 \hbar^3} \int_0^{+\infty} T(E_x) \ln(1 + e^{-(E_x - E_f)/kT}) dx \quad (5.74)$$

where $T(E_x)$ can be computed using the WKB approximation.

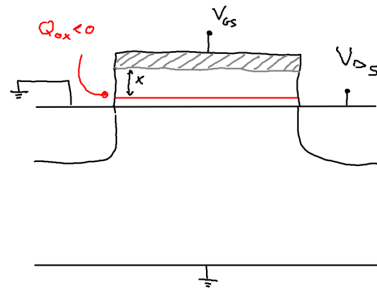
In particular under Foulner-Nordheim tunneling

$$J = AF_{ox}^2 e^{-B/F_{ox}} \quad (5.75)$$

Increasing the field in the oxide we enter in the direct tunneling regime being the boundary condition $F_{ox} = \frac{q\xi_s}{t_{ox}}$. Typical values are around $J=1 \text{ A/cm}^2$.



5.11.4 Charge in the oxide



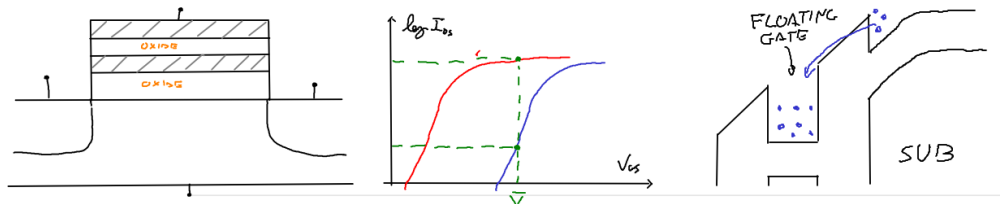
We will consider a sheet of negative charge in the oxide at distance x from the gate. In MOS-capacitor we recover the ideal behaviour with the application of an extra voltage on the gate of

$$\Delta V_g = -\frac{Q_{ox}}{C_{xg}} \quad (5.76)$$

this consideration is also good for MOS-transistor. We have only a rigid shift of the transcharacteristic by an amount ΔV_{gs} that will be rightward if the charge is negative or leftward if positive.

This phenomena is used adding a strate of poly-silicon in the oxide called floating gate like in figure.

Depending at the charge given at a certain \bar{V} we get different values of current. The charge in the floating gate is changed by quantum mechanical tunneling or other processes.



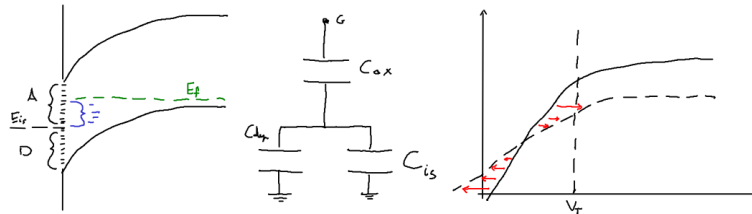
5.11.5 Interface states

We get the same consideration of the MOS-capacitor.

Now the change of charge at the surface is modulating the slope of the sub-threshold slope. It's like having another capacitance in parallel with C_{dep} so

$$STS = \frac{kT}{q} \ln(10) \left(1 + \frac{C_{dep} + C_{i,s}}{C_{ox}} \right) \quad (5.77)$$

We don't have a stretch of the characteristic when $E_f = E_{i,s}$



5.12 Short channel devices

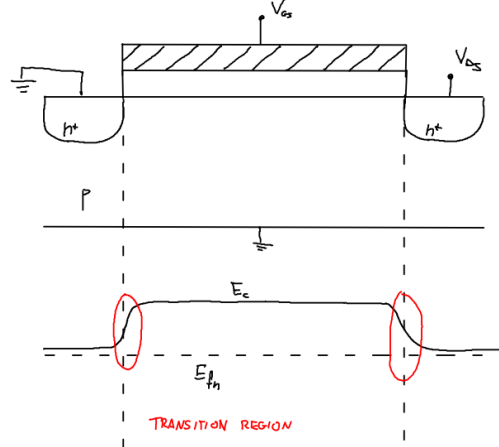
Reducing L we can increase the number of components per unit area and so decrease the costs per component and logic function. Furthermore

$$I_{ds} \propto \frac{W}{L} \quad C \propto WL \quad \rightarrow \quad \frac{I_{ds}}{C} = \frac{dV}{dt} \propto \frac{1}{L^2} \quad (5.78)$$

If we start reducing L leaving all the other parameters unchanged (like the oxide thickness or the doping concentrations) at the beginning the performance will increase but after a while they will become worst; this because some secondary effects becomes dominants degrading the good performance of the transistor.

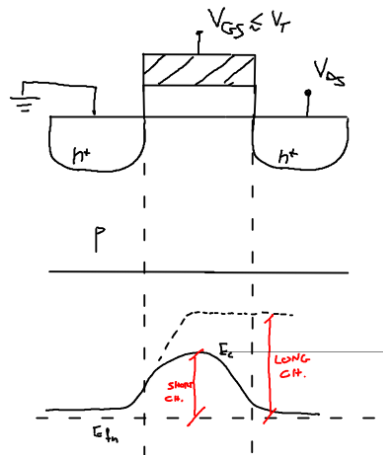
5.12.1 2D electrostatic in channel coming from n^+ regions

In a long channel device with drain bias equal to 0 and $V_{gs} \lesssim V_t$ bands are flat in the channel and the electron concentration is negligible.



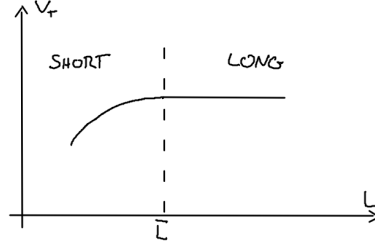
In our analysis we've always neglected the presence of the source and drain regions (that until now only setted the value of E_{fn} at the boundary of the channel). We have 2 transition regions that we have neglected because L is long and the thickness of this 2 region is negligible wrt L so they had a negligible impact.

If we reduce only L the electrostatics of the channel changes ; E_c rises but not as much as before because there is the influence of the drain transition region. We have everywhere an impact of the electrostatic of the source and drain regions we don't have a zone that can be controlled only by the gate.

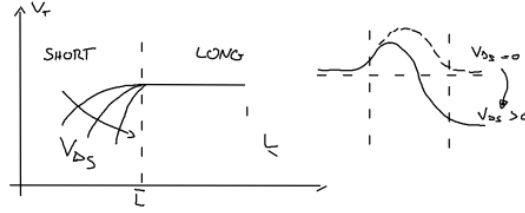


There are relevant electric field in y direction (gradient of E_{fn}) so an intrinsically 2D electrostatic.

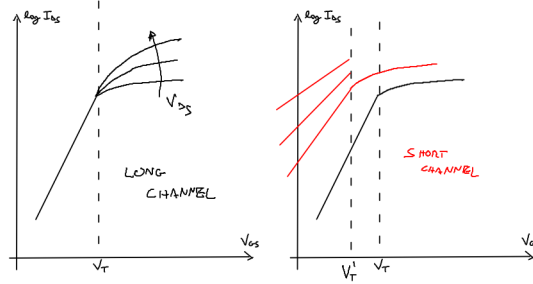
The distance $E_{fn} - E_c$ is narrower than before so we have more electrons that means we are reducing the V_t ; this effect is called the short channel effect. Transistor with different L have different V_t . Variability on L will reflect on variability in V_t .



If now we increase V_{ds} in short channel we change the electrostatic and the band bending moving E_c^{max} to a lower value and near to the source as in figure.



We are further reducing the V_t of the transistor; this phenomena is called drain induced barrier lowering or DIBL. The effect is a decrease of the output resistance in the saturation regime. In the transcharacteristic changing V_{ds} we change V_t increasing the on-state current exponentially and we have also a worsening of the STS that has a flatter dependance beacuse increasing V_{ds} we decrease the barrier and F_x becomes negligible wrt F_y .



This goes on until we have no barrier at all the gate is no more able to turn off the device; this condition is called punch-through regime.

From the 2D Poisson equation we get that the difference of V_t wrt a long channel device is

$$\Delta V_t = \frac{24t_{ox}}{W_d^{max}} \left(\sqrt{\phi_b(\phi_b - V_{ds})} - 0.4 \cdot 2|\phi_b| \right) e^{-\pi L/2(W_d^{max} + 3t_{ox})} \quad (5.79)$$

the importat term is the exponential.

To have a $\Delta V_t < 100mV$ we need to have

$$L > 2(W_d^{max} + 3t_{ox}) \quad (5.80)$$

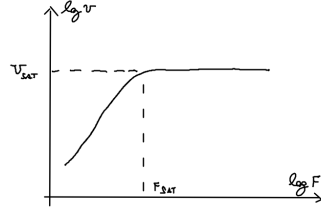
if this condition is respected we have a long channel device if not a short channel. So we don't have an absolute value but a dependance with t_{ox} , N_a to separate long and short channel mosfets.

Reducing t_{ox} we get a better control of the gate on the substate. With higher doping concentration the transitions regions are smaller but we get also a worst STS.

5.12.2 Velocity saturation

Now let's forget about previous effects seen for short channel devices (we're making a sort of sovrapposition of effects).

Reducing L we are increasing F but at very high F we the relation between the electric field and the drift velocity isn't linear ; at fields of $10^4 V/cm$ the velocity of electrons saturates at a value of $10^7 cm/s$.

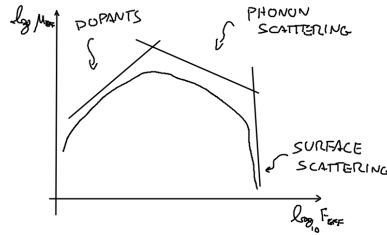


To express this dependence we can use the following formula

$$v_d = \mu_{eff} \frac{F}{[1 + \left(\frac{F}{F_{sat}}\right)^n]^{1/n}} \quad (5.81)$$

where n is a coefficient equal to 1 for holes in a p-mos, 2 for electrons in n-mos.

The term μ_{eff} it's an effective mobility and depends on F_x ; since the transport of electrons is very close to the surface there is a strong interaction with the interface Si-Oxide that causes surface-scattering events. The mobility in that region is much lower than that in the bulk and depends a lot on the vertical fields. We introduce also an effective vertical electric field as $F_{eff} = \frac{Q_{dep} + 0.5Q_{inv}}{\epsilon_{si}}$ that is related to the effective mobility as in the graph.



Now for the sake of simplicity we will consider $n=1$ in n-mos. We want to introduce velocity saturation expression in the current $I_{ds} = -\mu_n W Q_{inv} dV/dy$. Taking into account only the on-state regime we know that $V_s = 2|\phi_b| + V$ and so that $dV_s/dy = dV/dy = -F_y$ in strong inversion regime so we arrive at

$$\mu_n \frac{dV}{dy} = -\mu_n F_y = -v_d \quad \rightarrow \quad I_{ds} = W Q_{inv} v_d \quad (5.82)$$

So now we can introduce the velocity saturation equation in the expression (attention at the denominator we want a positive number so we take $|F|$)

$$I_{ds} = -W Q_{inv} \frac{\mu_{eff} \frac{dV}{dy}}{1 + \frac{1}{F_{sat}} \frac{dV}{dy}} \quad (5.83)$$

making some simple calculations we can write this equation like

$$I_{ds} = -[\mu_{eff} W Q_{inv} + \frac{I_{ds}}{F_{sat}}] \frac{dV}{dy} \quad (5.84)$$

We can take dy to the first member and integrate from 0-L and from 0- V_{ds} ; by assuming the quasi-1D model the only term that we really have to integrate is Q_{inv} that we can write like $Q_{inv} = -C_{ox}(V_{gs} - V_t - mV)$. Solving the integral we get

$$I_{ds} = \frac{\mu_n C_{ox} \frac{W}{L} [(V_{gs} - V_t)V_{ds} - \frac{mV_{ds}^2}{2}]}{1 + \frac{1}{F_{sat}} \frac{V_{ds}}{L}} \quad (5.85)$$

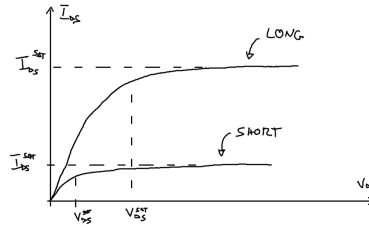
We get the same expression of the ideal case but with the denominator that scales the current. With L long the denominator $\simeq 1$.

Decreasing L we get a decrease of the current wrt the long channel case.

This relation has got a maximum at

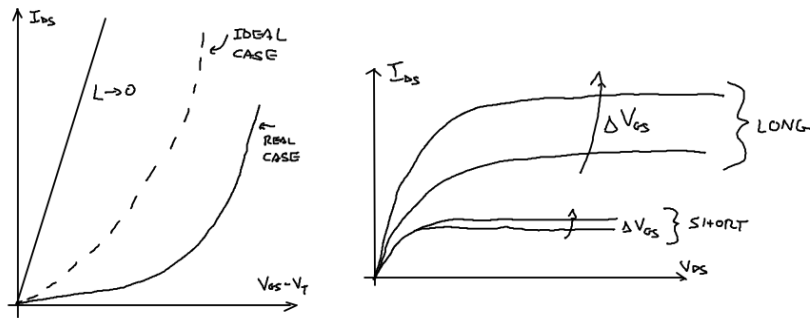
$$V_{ds}^{sat} = \frac{2(V_{gs} - V_t)/m}{1 + \sqrt{1 + \frac{2(V_{gs} - V_t)}{F_{sat}mL}}} \quad (5.86)$$

so we are reaching the saturation regime before than a long channel device and we get a higher slope of the rect after that point (Early's rect, this is also caused by the DIBL). With a short L we get lower saturation voltage and saturation current.



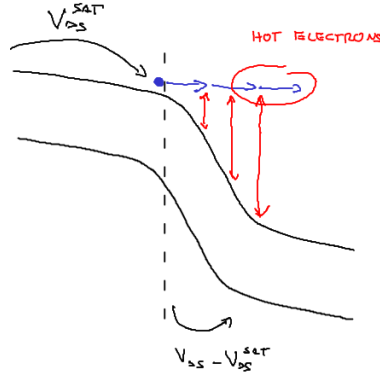
If we consider the inversion charge at the drain interface at V_{ds}^{sat} in a short channel device isn't zero we have still strong inversion. Before reaching pinch-off point at the drain we reach the saturation velocity; this 2 processes can lead our transistor in saturation region.

Ideally with shorter L we expect a steeper parabola in the transcharacteristic but we get considering the velocity saturation we get a high error. In an extreme case with $L \rightarrow 0$ $I_{ds}^{sat} \simeq WC_{ox}(V_{gs} - V_t)v_d^{sat}$ we get a linear dependance with V_{gs} and we get a lower sensitivity of the current to gate changes.



Hot electrons

The saturation velocity v_{sat} is the maximum average velocity in a drift-diffusion framework and so with scattering events. We can avoid scattering events by using steeper band banding.



Electrons that before scattering reaches a lot of kinetics energy (2-3eV) are called hot electrons. This electrons are so full of energy that can create impact ionization with atoms and so GR processes.

They can also inteact with silicon atoms at the surface breaking bonds and so creating some interface states. They are able to overcome the barrier of the oxide and reach the gate or remain trapped in the oxide (they are used for floating gates charge processes).

5.13 Scaling rules

There are some sets of scaling rules that we can take as guideline to scale our devices.

5.13.1 Constant field (Dennard)

Main idea is to avoid the 2D electrostatic regime keeping the ratio between the vertical and the horizontal fields constant $F_x/F_y = const.$

In order to do this we need to scale all vertical and horizontal dimensions of the same factor as the voltages.

For the doping concentrations we can say form the 2D Poisson equation in sub-threshold regime that

$$\frac{\partial^2 \phi}{\partial x^2} + \frac{\partial^2 \phi}{\partial y^2} = \frac{qN_a}{\epsilon_{si}} = -\frac{\partial F_x}{\partial x} - \frac{\partial F_y}{\partial y} \quad (5.87)$$

and so scaling all dimension by a factor k we get that to have the same electrostatic conditions

$$\frac{qN'_a}{\epsilon_{si}} = -\frac{\partial F_x}{\partial x/k} - \frac{\partial F_y}{\partial y/k} = -k \frac{\partial F_x}{\partial x} - k \frac{\partial F_y}{\partial y} \quad (5.88)$$

from wch we get that $N'_a = kN_a$ so the doping concentrations must increase by a factor k.

So the rules for constant fields scaling are

- Dimensions $(L, W, t_{ox}, X_j) \rightarrow \cdot 1/k$
- Voltages $(V_{gs}, V_{ds}, V_{bs}) \rightarrow \cdot 1/k$
- Doping concentrations $(N_a, N_d) \rightarrow \cdot k$

Device parameters changes

Electric field remains constant as the carriers velocity.

Capacitances scale as $1/k$.

Taking into account the drain current in parabolic regime $I_{ds} = \mu_n C_{ox} \frac{W}{L} [(V_{gs} - V_t)V_{ds} - \frac{mV_{ds}^2}{2}]$ the current is scaled as $1/k$ but we have to consider the V_t dependance. The threshold voltage has to be reduced by a factor k in accord with the second rule but we know that

$$V_t = V_{fb} + 2|\phi_b| + \frac{\sqrt{2\varepsilon_{si}qN_a2|\phi_b|}}{C_{ox}} \quad C_{ox} \rightarrow \cdot k \quad N_a \rightarrow \cdot k \quad (5.89)$$

but $2|\phi_b|$ does not scale by a factor k we have a logarithmic dependance on the doping concentration ($2|\phi_b| = kT/q \ln(N_a/n_i)$). We are not free to modify as we want V_t that is related with the energy gap and on $2|\phi_b|$. To overcome this we have to use non-constant doping concentrations.

The width of the depletion layer $W_d = \sqrt{\frac{2\varepsilon_{si}}{q} \frac{1}{N_a} 2|\phi_b|}$ do not scale with k but less for it's dependance with $2|\phi_b|$. So scaling the device with this set of rules we are slowly moving to the short channel regime according to the formula

$$L > 2(W_d^{max} + 3t_{ox}) \quad (5.90)$$

because L scales as $1/k$, t_{ox} scales as $1/k$ but due to the dependance of W_d^{max} on $2|\phi_b|$ it scales less than $1/k$.

Scaling also V_t of k (supposing it possible) since the scaling process does not affect the STS we are exponentially increasing the off-power dissipation.

The transit time $\tau = L^2/(\mu_{eff}V_{ds})$ is scaled of $1/k$ so we are getting a better frequency response.

Circuit parameters changes

Delay of logic gates:

CV/I_{ds} capacitances, current and voltage scale as $1/k$ so we get that the delay of logic gates decreases by a factor $1/k$.

Power dissipation:

VI_{ds} both scale as $1/k$ so the power dissipation scales as $1/k^2$ we have less dissipated power per logic function.

Density of power dissipation:

$\frac{VI_{ds}}{WL}$ the power dissipated per unit area remains constant (but we have more logic function in that area)

Integration density:

$1/WL$ number of device per unit area increase by a factor k

The negative aspects of this set of scaling rules are that we are slowly moving to short channel regime, we have higher off-power dissipation and we lose compatibility to one technology to the other scaling the voltages.

5.13.2 Generalized scaling rules (Baccarjni)

We accept an increase of F in order to move away from the 2D electrostatic regime (moving near to the velocity saturation regime).

With the same path of before we define the 3 rules of this set

- Dimensions $(L, W, t_{ox}, X_j) \rightarrow \cdot 1/k$
- Voltages $(V_{gs}, V_{ds}, V_{bs}) \rightarrow \cdot \alpha/k$
- Doping concentrations $(N_a, N_d) \rightarrow \cdot \alpha k$

with $1 < \alpha < k$

Parameters change

Carrier velocity:

In the case of linear or low field regime $\cdot \alpha$, in velocity saturation $\cdot 1$.

Current:

In low field $\cdot \alpha^2/k$, in velocity saturation $\cdot \alpha/k$.

Capacitances:

The electric field is not involved so we get $1/k$ for every regime.

Delay of logic gates:

In low field $\cdot 1/k$, in saturation $\cdot 1/k$.

Power dissipation:

In low field $\cdot \alpha^3/k$, in saturation $\cdot \alpha^2/k$.

Density of power dissipation:

In low field $\cdot \alpha^3/k^2$, in saturation $\cdot \alpha^2/k^2$ (we get problems from heat dissipation).

Increasing the doping concentration of more than k we get that W_d^{max} decreases more so we don't reach short channel regime.

With $\alpha = k$ we keep the same voltages and so compatibility with the older processes.

Increasing F we are increasing hot electrons that can tunnel through the gate that is becoming thinner so we get an exponential increase of the gate current with this process. In order to avoid this we use high- k material instead of SiO_2 increasing the thickness of the oxide but preserving the same capacitance so

$$t_{ox}^{hk} = \frac{\varepsilon_{hk}}{\varepsilon_{ox}} t_{ox} \quad (5.91)$$

However high- k materials are not so good in terms of charge inside the oxide, spurious states and interface states wrt SiO_2 .

5.14 Constraint on electrical parameters

We know the formula for the STS that can be written as

$$STS = 60 \frac{mV}{dec} \cdot m = 60 \frac{mV}{dec} \cdot \left(1 + \frac{C_{dep}}{C_{ox}}\right) \quad (5.92)$$

We want a low STS and so an $m \simeq 1$. Taking as upper limit $STS < 85 \frac{mV}{dec}$ we get $m < 1.4$ data from which we can elaborate the following formula

$$m = 1 + \frac{C_{dep}}{C_{ox}} = 1 + \frac{\varepsilon_{Si} t_{ox}}{\varepsilon_{ox} W_d^{max}} \rightarrow t_{ox} < 0.13 W_d^{max} \quad (5.93)$$

We started from an electrical constraint to arrive to a physical parameter.

Referring to a long channel behaviour we can refer to the condition of

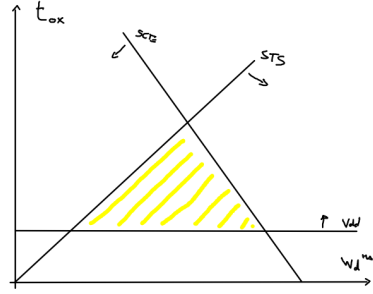
$\Delta V_t^{short\ channel\ effect} = [...]e^{-\frac{\pi L}{2(W_d^{max} + 3t_{ox})}} < 100mV$ from this we get the well known equation $L > 2(W_d^{max} + 3t_{ox})$ that we can write to highlight the oxide thickness as

$$t_{ox} < \frac{L}{6} - \frac{W_d^{max}}{3} \quad (5.94)$$

Another constraint is the maximum electric field in the oxide so $\frac{V_{dd}}{t_{ox}} < F_{ox}^{max}$ and so

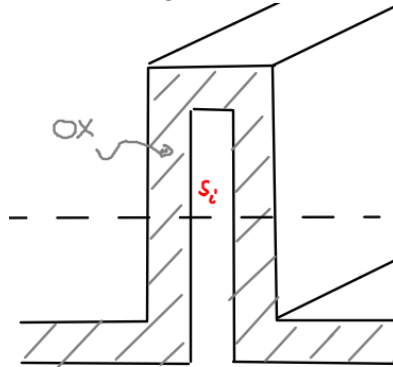
$$t_{ox} < \frac{V_{dd}}{F_{ox}^{max}} \quad (5.95)$$

We can study this 3 constraint on t_{ox} in a graph $t_{ox} - W_d^{max}$

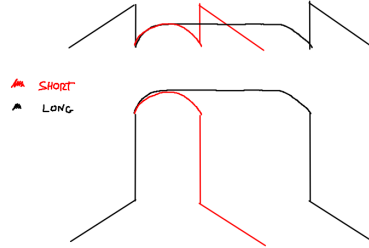


To satisfy the 3 requirements we have to stay in the triangle area and so we have a minimum and a maximum value for t_{ox} . In particular $t_{ox}^{max} \simeq \frac{L}{20}$; scaling L we have also to scale the oxide thickness increasing the leakage current through the gate.

Of course in the graph $t_{ox}^{max} > t_{ox}^{min}$ that means $V_{dd} < \frac{L F_{ox}^{max}}{20}$ but reducing the supply voltage we have also to reduce V_t and doing so we increase the off-state current and power dissipation. From a requirement on off-power dissipation we can get the $I_{off} = I_{ds}^{V_{ds}=V_{dd}, V_{gs}=0}$ and from sub-th current get the V_t we want. We have to take the worst case so the one at high temperature and then come back to the RT. Also we can't increase too much V_t or the on-state current will be too low. Typical requirement is to have $V_t \leq \frac{V_{dd}}{4}$. These constraints are why we came to "strange" structure like the finfet in figure



where we have a 3D channel controlled in a more strong way beacuse the gate wraps around the substrate over 2 dimensions having so a better STS and a volume inversion charge. If we look at the band diagram in the crossection with t_{si} large and small we can say that shorter the silicon thickness is better control of the substrate we have.

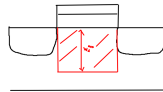


5.15 Moore's Law and problems in the "too small"

Moore's law :number of components per chip doubles every 2 years and so beacuse the area remains constant we get an integration density reduction of a factor $\sqrt{2}$ so we get

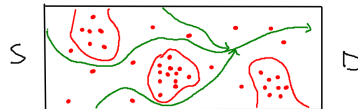
$$45nm \rightarrow 32nm \rightarrow 22nm \rightarrow 14nm \rightarrow 10nm \quad (5.96)$$

With so small spaces we have problems of statistical variability due to the intrinsic discrete nature of atoms; dopants are point charge not concentrations.



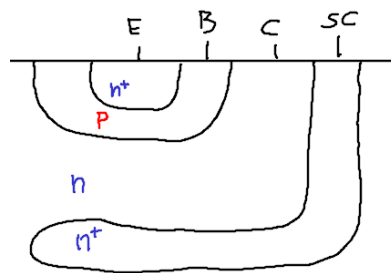
In the area under the gate of a mos we have a certain nuber of dopants that can be calculated as $M = N_a W L W_d^{max}$ that for a 10nm thecnology are of a few thousand so variation of this number are very important and effective on the device behaviour.

Also with so few M it's relevant the position of them; we can have regions where the local V_t is higher causing a non uniform inversion layer ad so a percolative substrate conduction.



Chapter 6

BJT



This device is created with 2 pn junctions with a back to back connection creating a npn or a pnp device. This device can be horizontal or vertical (we will study this second approach because it is the most important).

The n structure is the collector, the adjacent n^+ part is the sub-collector region connected to the surface with a reach-through implantation. The current flows in the vertical direction so the most significant part is the one under the emitter area.

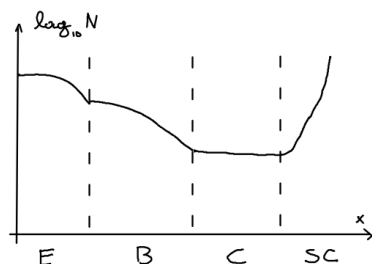
The main idea is to forward bias the EB-j and reverse bias the BC-j. Forward bias in EB-j so there will be a flow of electrons from E to B and holes from B to E but if the base region is narrow we have that electrons don't recombine in the p region but travel through it reaching the collector. We have a large flow of electrons through a reverse biased junction (BC) because the supply comes from the EB-j and not from GR processes. In the collector we have high resistivity due to low doping concentrations so we have to put the sub-collector to make a contact.

This device has a significant flow of both electrons and holes so it's a bipolar device (intrinsic flow of holes from base to emitter).

We can minimize the base current by reducing the width of the base (to avoid recombination of e, so that they can reach the collector) and also making the emitter more doped wrt the base (since the dominant current flow comes from the zone less doped doing so the holes from the emitter will be less).

If the BC-j was direct biased we will have an additional component to the base current that is something we want to avoid.

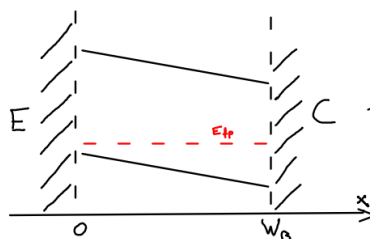
6.1 Doping concentrations



Let's analyse the doping concentrations; in emitter region we have high doping concentration $N_d^E \simeq 10^{20}$ that decrease until 10^{18} , the base from $N_a^B = 10^{18}$ to 10^{17} and then the collector and the subcollector as in figure. The non constant doping concentration is relevant in the operation of the device.

6.2 Collector current

We can focus our analysis on the quasi-neutral p region that is the bottom-neck for conduction of the system.



We call W_b the quasi neutral region of the base. In this region the band bending is set by holes concentration.

Doping concentration is not constant so we have band bending and an electric field. This condition can be reached also with high level of injection.

Considering hole concentration $p = n_i e^{\frac{E_i - E_{fp}}{kT}}$ we get $E_i = E_{fp} + kT \ln(p/n_i)$. We want this parameter because it's related to the potential and so to the electric field

$$F = -\frac{d\phi}{dx} = \frac{1}{q} \frac{dE_i}{dx} = \frac{1}{q} \frac{dE_{fp}}{dx} + \frac{kT}{q} \frac{1}{p} \frac{dp}{dx} \quad (6.1)$$

both high injection and non constant doping concentration events are taken into account by the term $\frac{dp}{dx}$, the term $\frac{dE_{fp}}{dx}$ take into account of resistive drops.

The base current density is $J_B = p\mu_p \frac{dE_{fp}}{dx}$ so we get that $\frac{dE_{fp}}{dx} = J_B/(p\mu_p)$ and so putting this equation into the electric field equation we get

$$\frac{1}{q} \frac{J_B}{p\mu_p} + \frac{kT}{q} \frac{1}{p} \frac{dp}{dx} \quad (6.2)$$

using some reasonable values for all the parameter we get that ΔV_t is of a few fractions of mV when the total voltage applied is in the order of 0.6-0.7V. This contribution is negligible we

consider the E_{fp} almost constant so

$$F = \frac{kT}{q} \frac{1}{p} \frac{dp}{dx} \quad (6.3)$$

We can recover the drift-diffusion expression for the current and using F we get

$$J_n = qn\mu_n \frac{kT}{q} \frac{1}{p} \frac{dp}{dx} + qD_n \frac{dn}{dx} \quad (6.4)$$

We are in a quasi neutral region so $p(x) = N_a(x) + n(x)$ we can get 2 cases.

Low injection

$n \ll N_a$ so the expression for the current is

$$J_n = qn\mu_n \frac{kT}{q} \frac{1}{N_a} \frac{dN_a}{dx} + qD_n \frac{dn}{dx} \quad (6.5)$$

where $\frac{kT}{q} \frac{1}{N_a} \frac{dN_a}{dx}$ is the built in electric field due to non constant doping concentration.

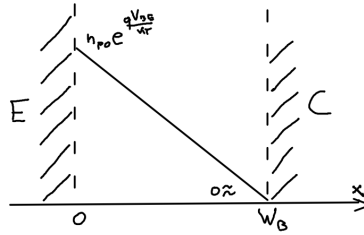
High injection

$n \gg N_a$ so we get

$$J_n = qn\mu_n \frac{kT}{q} \frac{1}{n} \frac{dn}{dx} + qD_n \frac{dn}{dx} = 2qD_n \frac{dn}{dx} \quad (6.6)$$

it's like a pure diffusion process with the double of the intensity; this is called the Webster effect.

6.2.1 Prototype BJT current



It's a super-ideal case where we have constant doping concentrations and low level of injection.

So we have that $J_n = qD_n \frac{dn}{dx}$; we can say as "boundary conditions" that $n(0) = \frac{n_i^2}{N_a} e^{qV_{BE}/kT}$

and that $n(W_b) = \frac{n_i^2}{N_a} e^{qV_{BC}/kT}$ but because $V_{BC} < 0$ we can say that $n(W_b) \simeq 0$.

Now we can integrate the two members and since J_n is a constant because there isn't recombination we get

$$J_n = qD_n \frac{n(W_b) - n(0)}{W_b} \quad (6.7)$$

that is legit because $\frac{dn}{dx}$ it's a linear profile we are considering a narrow base diod.

$$J_n = -\frac{qD_n n_i^2}{N_a W_b} e^{qV_{BE}/kT} \quad (6.8)$$

We can now multiply for the area of the emitter A_E and add a minus sign because we want current positive if flows into the collector arriving at

$$I_c = A_E \frac{qn_i^2}{N_a W_b} e^{qV_{BE}/kT} = A_E \frac{qn_i^2}{G_B} e^{qV_{BE}/kT} \quad (6.9)$$

where $G_B = \frac{N_a W_b}{D_n}$ it's the Gummel number of the base. This current it's dependent only on base parameters.

6.2.2 "Ideal" BJT

We consider now the possibility of non constant doping concentration or high injection regime so we recover the expression $J_n = qn\mu_n \frac{kT}{q} \frac{1}{p} \frac{dp}{dx} + qD_n \frac{dn}{dx}$ that we can write as

$$J_n = \frac{qD_n}{p} \left(n \frac{dp}{dx} + p \frac{dn}{dx} \right) = \frac{qD_n}{p} \frac{d(pn)}{dx} \quad (6.10)$$

As before we integrate keeping J_n as a constant (neglecting G-R and in stationary conditions) we know that $pn(W_d) \simeq 0$ so we reach the current density as

$$J_n = - \frac{qn_i^2}{\int_0^{W_b} \frac{p}{D_n} dx} e^{qV_{BE}/kT} \quad (6.11)$$

If we multiply for the emitter area and change sign we get the collector current as

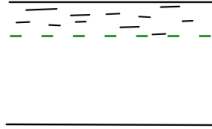
$$I_c = A_E \frac{qn_i^2 e^{qV_{BE}/kT}}{\int_0^{W_b} \frac{p}{D_n} dx} = A_E \frac{qn_i^2 e^{qV_{BE}/kT}}{G_B} \quad (6.12)$$

where $G_B = \int_0^{W_b} \frac{p}{D_n} dx$ is the new Gummel number for the base that in case of constant doping and low level of injection becomes the first one.

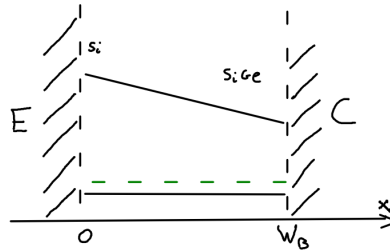
6.2.3 Real BJT

The most general case we can include the non-constant bandgap in the base. We can have a non constant bandgap due to 2 causes.

The first cause of bandgap narrowing is due to doping concentrations that are higher than $\simeq 10^{18}$; high doping means donor closer to each other interaction between energy levels that becomes a band of energy and some of this level can overlap the E_c narrowing the band-gap. The emitter side we will have a narrower gap than the collector side.



Second cause is a technological method to gradually change from Si to GeSi to narrow the bandgap ($E_{gap}^{Ge} < E_{gap}^{Si}$).



We have an important role of the bangap only in $pn = n_i^2 e^{(E_{fn} - E_{fp})/kT}$ in this case the intrinsic carrier concentration becomes

$$n_{i,e}^2 = N_v N_c e^{-E_{gap}/kT} e^{\Delta E_{gap}/kT} = n_i^2 e^{\Delta E_{gap}/kT} \quad (6.13)$$

where $n_{i,e}$ is the effective intrinsic carrier density. So $J_n = n \mu_n \frac{dE_{fn}}{dx}$ where from the previous equation and the generalized law of mass action we get

$$pn = n_{i,e}^2 e^{\frac{E_{fn} - E_{fp}}{kT}} \quad (6.14)$$

$$E_{fn} = E_{fp} + kT \ln\left(\frac{pn}{n_{i,e}^2}\right) \quad (6.15)$$

considering E_{fp} constant as usual we get that the current density is

$$J_n = -qD_n \frac{n_{i,e}^2}{p} \frac{d(pn/n_{i,e}^2)}{dx} \quad (6.16)$$

as the previous case now we integrate this expression

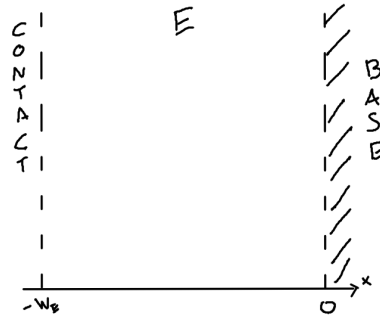
$$J_n = -\frac{q e^{qV_{BE}/kT}}{\int_0^{W_b} \frac{p}{D_n n_{i,e}^2} dx} \quad (6.17)$$

Multiplying the result for the emitter area and changing the sign we get the collector current as

$$I_c = A_E \frac{q n_i^2 e^{qV_{BE}/kT}}{\int_0^{W_b} \frac{n_i^2 p}{n_{i,e}^2 D_n} dx} = A_E \frac{q n_i^2 e^{qV_{BE}/kT}}{G_B} \quad (6.18)$$

6.3 Base current

Base current created by holes that moves from base to emitter region. In our analysis we will consider emitter region beacuse it's the bottom neck for conduction in this process.



6.3.1 Shallow emitter

We can neglect recombination of holes and so $J_p = \text{const.}$

We will refer to the most general case of high level of injection, non constant doping concentration and gap narrowing.

From the consideration made for the collector current we get $J_p = -qD_p \frac{n_{i,e}^2}{n} \frac{d(pn)}{dx}$ and as boundary condition we know that $p(0) = p_{n0} e^{qV_{BE}/kT}$ and at the contact $p(-W_e) = p_{n0}$.

Making one step of integration (and neglecting 1) we get

$$J_p = -qe^{qV_{BE}/kT} \frac{1}{\int_{-W_e}^0 n/(qD_n n_{i,e}^2) dx} \quad (6.19)$$

From this we get the base current

$$I_B = qA_E e^{qV_{BE}/kT} \frac{n_i^2}{\int_{-W_e}^0 \frac{nn_i^2}{n_{i,e}^2 D_n} dx} = qA_E e^{qV_{BE}/kT} \frac{n_i^2}{G_E} \quad (6.20)$$

where G_E is the Gummel number of the emitter. All base current parameter are function of the emitter.

We will never reach high injection condition beacuse the emitter is highly doped so we can write

$$G_E = \frac{N_d^E n_i^2}{n_{i,e}^2 D_n} W_B \quad (6.21)$$

6.3.2 Deep emitter

In the case of constant doping an low level of injection from pn-j results neglecting -1 we get

$$J_p = -\frac{qD_p n_i^2}{N_d^E L_p \tanh(W_e/L_p)} e^{\frac{qV_{BE}}{kT}} \quad (6.22)$$

and so the base current as

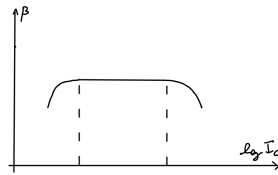
$$I_B = A_E \frac{qn_i^2}{\frac{N_d^E L_p \tanh(W_e/L_p)}{D_p}} e^{qV_{BE}/kT} = A_E \frac{qn_i^2}{G_E} e^{qV_{BE}/kT} \quad (6.23)$$

where $G_E = \frac{N_d^E L_p \tanh(W_e/L_p)}{D_p}$ it's the new Gummel number of the emitter.

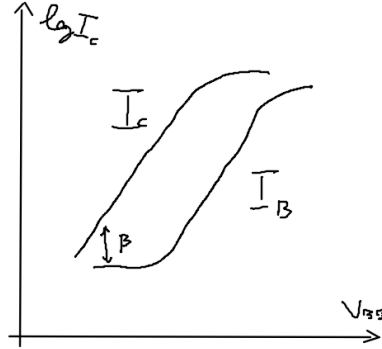
Now we can calculate the beta of the transistor as

$$\beta = \frac{I_C}{I_B} = \frac{G_E}{G_B} \quad (6.24)$$

6.4 β dependance on I_C



β changes with different I_C values at high current and low current we can see a drop of this parameter.



Plotting the Gummel plot for the BJT that at low current the base current drops slowly reducing β while at high current both I_C and I_B deviate from ideal characteristic.

At low current we have GR processes of the forward biased EB junction in the depletion layer.

At high currents we have high injection effects and resistive drops.

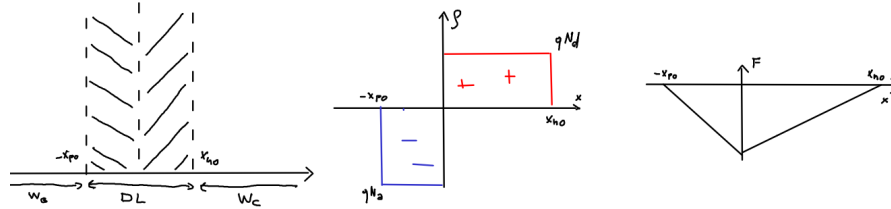
The high injection effects affect only I_C for the low doping of the base region. This is called modulation of the base conductivity.

6.5 Kirk effect

Consider now the BC junction under the condition of constant doping concentration. We get the results of a pn junction.

The total charge in the quasi neutral region is 0 but in the depletion zone we have some localized charge and so an electric field as shown in the figures below.

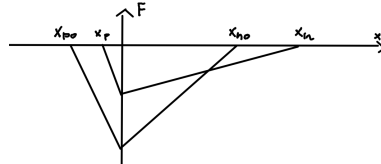
The area of the triangle of F profile has to be constant and proportional to $\Delta\phi = \phi_{bi} + V_{CB}$.



All this results are based on the depletion approximation but in this case we have the EB-j that forces a large (and independent on V_{BC}) flow of electrons.

Electrons move by drift (we are in a reverse bias junction) and we can suppose they move at the saturation velocity so $J_n = qnv_{sat}$ from which we can write that $n = J_n/qv_{sat}$; if J_n increase also n increase until it's comparable with N_d^C and in this case the depletion approximation is no more valid.

The slope of the second part of F becomes from $\frac{qN_d^C}{\epsilon_{si}}$ to $\frac{q(N_d^C - n)}{\epsilon_{si}}$ we are reducing the slope but the area has to remain constant so we decrease also the electric field.



We have so doing a wider W_B the Gummel number of the base increase and so the collector current decreases.

This is called Kirk effect and does not affect the base current.

In the beginning case we can say that $x_{p0}N_a^B = x_{n0}N_d^C$ and from this that

$$W_{d0} = \sqrt{\frac{2\varepsilon_{Si}}{q} \Delta\phi \left(\frac{1}{N_a^B} + \frac{1}{N_d^C} \right)} \quad \Delta\phi = W_{d0}^2 \frac{q}{2\varepsilon_{Si}} N_a^B // N_d^C \quad (6.25)$$

but when we have non negligible n we get $x_{p0}(N_a^B + n) = x_{n0}(N_d^C - n)$ and from that

$$\Delta\phi = W_{d0}^2 \frac{q}{2\varepsilon_{Si}} \frac{(N_a^B + n)(N_d^C - n)}{N_a^B + N_d^C} \quad (6.26)$$

combining this 4 equations we get the real distances

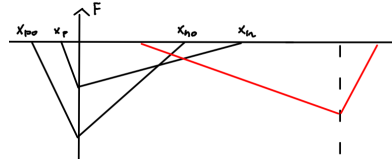
$$x_n = x_{n0} \sqrt{\frac{1 + n/N_a^B}{1 - n/N_d^C}} \simeq \frac{x_{n0}}{\sqrt{1 - n/N_d^C}} \quad (6.27)$$

$$x_p = x_{p0} \sqrt{\frac{1 - n/N_d^C}{1 + n/N_a^B}} \simeq x_{p0} \sqrt{1 - n/N_d^C} \quad (6.28)$$

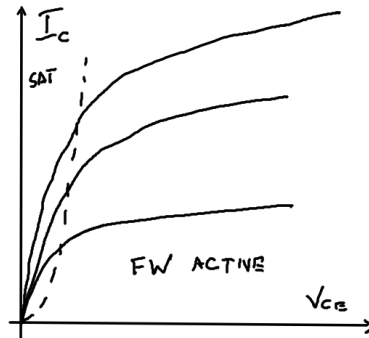
We can increase more the quasi-neutral base region. If we keep increasing n we arrive that the depletion layer in the collector reaches the subcollector (where it stops for high doping of this region) like in the graph.

Increasing more the depletion layer moves to the C-SC junction making W_B a lot wider and so having a drop of β and of the frequency response.

The onset of this event can be found at current $J_n = qnv_{sat} = qN_d^C v_{sat}$



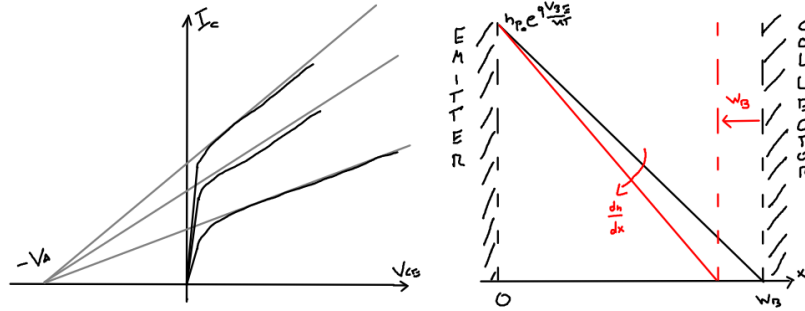
6.6 Early effect



Now we want to investigate the dependences of I_C on V_{CE} so we focus on the qn base region and we keep V_{BC} not big and negative.

If $V_{CE} = 0$ than $V_{BE} = V_{BC}$ so constant electron concentration and no diffusion current (accounting for base current it isn't really zero but slightly negative). Increasing V_{CE} we reduce forward bias on BC decrease electron concentration at the BC depletion region so the current increase and we enter in the forward active mode leaving the saturation regime.

In the forward active mode we have a slight increase of the current the physical reason for this comes from the qn region of the base; increasing V_{CE} at constant V_{BE} we are moving the width of the depletion layer in the base increasing F profile and so the diffusion current. This is the Early effect of the BJT.



We follow the rect until the interception with the x axes where we find $-V_A$ the Early voltage. The slope of the rect is $\frac{\partial I_C}{\partial V_{CE}}$ given a certain \hat{I}_C, \hat{V}_{CE} we can say that $\frac{\partial I_C}{\partial V_{CE}} = \hat{I}_C / (V_A + \hat{V}_{CE})$ and so neglecting \hat{V}_{CE} that is small

$$V_A = \frac{\hat{I}_C}{\frac{\partial I_C}{\partial V_{CE}}} \quad (6.29)$$

we can say that $\frac{\partial I_C}{\partial V_{CE}}|_{V_{BE}} = \frac{\partial I_C}{\partial V_{CB}}$ and so

$$\frac{\partial I_C}{\partial V_{CB}} = -\frac{\hat{I}}{W_B} \frac{\partial W_B}{\partial V_{CB}} \quad (6.30)$$

where

$$\frac{\partial W_B}{\partial V_{CB}} = -\frac{\partial x_{p0}}{\partial V_{CB}} \frac{q N_a^B}{q N_a^B} = -\frac{C_{dep}^{BC}}{q N_a^B} \quad (6.31)$$

where the minus sign is for coherence with the prototype transistor current. Finally we get

$$V_A = \frac{q N_a^B W_B}{C_{dep}^{BC}} = \frac{Q_p}{C_{dep}^{BC}} \quad (6.32)$$

Q_p total base charge of holes.

To increase V_A we have 3 factors that we can modify: N_a , C_{dep}^{BC} and the width of the base (that regulates W_B).

An increase of N_a^B degenerates the β of the transistor and a larger W_b means G-R processes in the base so an extra base current and the decrease of the frequency response.

It's better to act on C_{dep}^{BC} ; reducing N_d^C we have a larger W_d and so a smaller capacitance but the triggering level for Kirk effect becomes lower.

The lower limit for the width of the base is to avoid the punch-through regime that is when the entire base is depleted.

6.7 Small signal model

6.7.1 Transconductance

Variation of I_C with a small variation of V_{BE} at constant V_{CE}

$$g_m = \left. \frac{\partial I_C}{\partial V_{BE}} \right|_{V_{CE}} = \frac{I_C}{kT/q} \quad (6.33)$$

6.7.2 Output resistance

Variation of I_C with variation of V_{CE} at constant V_{BE} to the minus one

$$r_0 = \left(\left. \frac{\partial I_C}{\partial V_{CE}} \right|_{V_{BE}} \right)^{-1} = \frac{V_A}{I_C} \quad (6.34)$$

6.7.3 Base resistance

How I_B change with small change of V_{BE} at constant V_{CE}

$$r_\pi = \left(\left. \frac{\partial I_B}{\partial V_{BE}} \right|_{V_{CE}} \right)^{-1} = \frac{\beta}{g_m} \quad (6.35)$$

Note that $\left. \frac{\partial I_B}{\partial V_{CE}} \right|_{V_{BE}} = 0$.

6.7.4 Capacitive effects

We have 2 capacitance $C_\pi = C_{dep}^{BE} + C_{diff}$, where C_{diff} comes from the modulation of free carrier charge inside the device, and $C_\mu = C_{dep}^{BC}$.

We only miss the value of C_{diff} . We can analyse first $Q_{diff} = Q_B + Q_E + Q_{BC} + Q_{BE}$ where Q_{BC} is for the Kirk effect Q_B, Q_E come from the quasi neutral region of the base and collector.

→ $Q_B = I_C t_b$ where t_b is the transit time of minority carriers. From pn junction's results we get that $t_b = W_b^2 / 2D_n$.

→ Considering a deep emitter we get $Q_E = I_B \tau_p = I_C \frac{\tau_p}{\beta} = I_C t_e$ where t_e time related to emitter region (not transit time of course).

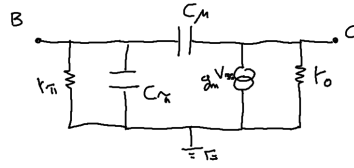
→ Q_{BC} free charge stored in BC depletion region that is

$$Q_{BC} = q \frac{J_n}{qv_{sat}} W_d^{BC} A_E = I_C \frac{W_d^{BC}}{v_{sat}} = I_C t_{BC} \quad (6.36)$$

→ For Q_{BE} we can't use the previous results beacuse we have diffusion process but we say it's $Q_{BE} = I_C t_{BE}$. It's a negligible contribution.

So $Q_{diff} = I_C(t_b + t_e + t_{bc} + t_{be}) = I_C \tau$ and finally

$$C_{diff} = \frac{\partial Q_{diff}}{\partial V_{BE}} = g_m \tau \quad (6.37)$$



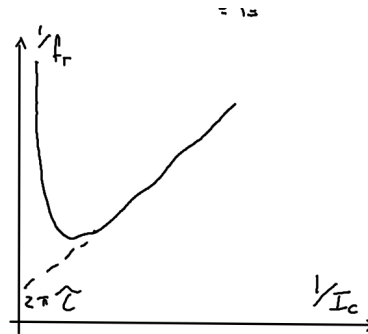
6.8 Frequency response

The cut off frequency is

$$f_t = \frac{g_m}{2\pi(C_\pi + C_\mu)} \quad (6.38)$$

having g_m means dependance on the collector current so we can make the invers of the equation and plot a graph to better understand the frequency response

$$\frac{1}{f_t} = \frac{2\pi(C_{dep}^{BE} + C_{dep}^{BC})}{I_C} \frac{kT}{q} + 2\pi\tau \quad (6.39)$$

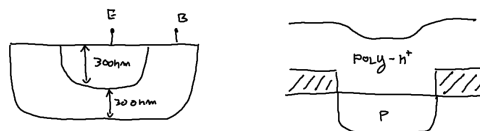


At too high current we enter in high current regime triggering base widening and Kirk effect that decrease our frequency response.

6.9 Considerations

If we want to increase I_C we have to increase N_d^C to avoid Kirk and work at higher frequency but to not worst the Early effect we have to increase also N_d^B but at this point also N_d^E to not decrease β .

We want low variability of β so a deep emitter with the consequents strange process technology as in figure.



We aren't able due to process tollerance to make an emitter deep 300nm and a base only 10nm they have to be of the same dimensions if we don't use particular pocesses like in the second

figure. With this method we can have a very deep emitter made of n^+ -polysilicon deposited at last and a shallow base that is doped as first process.

With this technology we can arrive at $f_t \simeq 100GHz$.

With C-mos technology we have to trade the maximum gain with high frequency regimes but in bjt technology no; this is why bjt's are still used for analog circuits.

In a simple amplifier with a BJT the maximum gain is $G_{max} = g_m r_0 = V_a / (\frac{kT}{q}) \simeq 1000$ that is independent on the working current. In a MOS amplifier we have $G_{max} = V_a / \left(\frac{V_{gs} - V_t}{m} \right) \simeq 100$ that is lower but we can also write that as

$$G_{max} = \sqrt{\mu_n C_{ox} W L / 2 m} \frac{F_P}{\sqrt{I_{ds}^{sat}}} \quad (6.40)$$

that shows us the trade off between maximum gain and frequency response.

...that's all for today see you tomorrow!

Chapter 7

Summary on basics formulas

7.1 Semiconductors basics

$$\phi = -\frac{E}{q} \quad (7.1)$$

$$F = -\frac{d\phi}{dx} \quad (7.2)$$

Diffusion coefficients

$$D_n = \mu_n \frac{kT}{q} \quad D_p = \mu_p \frac{kT}{q} \quad (7.3)$$

Debye length

$$L_D = \sqrt{\frac{\varepsilon_{Si} kT}{q^2 N_d}} \quad (7.4)$$

Current expressions

$$J_p = -qp\mu_p \frac{d\phi_{fp}}{dx} \quad (7.5)$$

$$J_n = p\mu_p \frac{dE_{fp}}{dx} \quad (7.6)$$

$$J_n = -qn\mu_n \frac{d\phi_{fn}}{dx} \quad (7.7)$$

$$J_n = n\mu_n \frac{dE_{fn}}{dx} \quad (7.8)$$

Equation for e and h

$$\frac{\partial n}{\partial t} = \frac{1}{q} \frac{\partial J_n}{\partial x} + G - R \quad \frac{\partial p}{\partial t} = -\frac{1}{q} \frac{\partial J_p}{\partial x} + G - R \quad (7.9)$$

Recombination R

$$R = \frac{pn - n_i}{\tau_0 [p + n + 2n_i \cosh(\frac{E_T - E_i}{kT})]} \quad (7.10)$$

7.2 Diodes

General current-carriers expression

$$J = [\frac{qD_n n_{p0}}{L_n \tanh(W_p/L_n)} + \frac{qD_p p_{n0}}{L_p \tanh(W_n/L_p)}](e^{\frac{qV}{kT}} - 1) = J_0(e^{\frac{qV}{kT}} - 1) \quad (7.11)$$

$$\Delta n(x) = n_{p0}(e^{\frac{qV}{kT}} - 1) \frac{\sinh(\frac{W_p - x}{L_n})}{\sinh(\frac{W_p}{L_n})} \quad (7.12)$$

For wide base diod we have

$$\Delta n(x) = n_{p0}(e^{\frac{qV}{kT}} - 1)e^{\frac{-x}{L_n}} \quad J_n = \frac{qD_n n_{p0}(e^{\frac{qV}{kT}} - 1)}{L_n} \quad (7.13)$$

For narrow base diod we have

$$\Delta n(x) = n_{p0}(e^{\frac{qV}{kT}} - 1)e^{\frac{-x}{L_n}} \quad J_n = \frac{qD_n n_{p0}(e^{\frac{qV}{kT}} - 1)}{L_n} \quad (7.14)$$

R-current

$$J_R = qR_{max}W_d = qW_d \frac{n_i(e^{\frac{qV}{2kT}})}{2\tau_0} \quad (7.15)$$

G-current

$$J_G = -q \frac{n_i}{2\tau_0} W_d \quad (7.16)$$

General low current expression due to G-R processes

$$J_{GR} = \frac{qn_i}{2\tau_0} W_d (e^{\frac{qV}{2kT}} - 1) = J_{0GR}(e^{\frac{qV}{2kT}} - 1) \quad (7.17)$$

7.3 Metal-semiconductor junction

Bethe's model current from semiconductor to metal

$$J_{s-m}^{(1)} = \frac{4\pi q}{h^3} \sqrt{m_x m_y} (kT)^2 e^{\frac{-\phi_{bn}}{kT}} e^{\frac{qV}{kT}} = A \cdot \sqrt{m_x m_y} T^2 e^{\frac{-\phi_{bn}}{kT}} e^{\frac{qV}{kT}} \quad (7.18)$$

Bethe's model current in MS-J

$$J = A^* T^2 e^{\frac{-q\phi_{bn}}{kT}} (e^{\frac{qV}{kT}} - 1) = J_{0,th}(e^{\frac{qV}{kT}} - 1) \quad (7.19)$$

Universal model boundary condition

$$J_n(0) = \frac{A^* T^2}{N_c} [n(0) - n_0] \quad (7.20)$$

Shottky effect barrier lowering

$$E_0(x) = E_0(+\infty) - \frac{q^2}{16\pi\epsilon_0 x} \quad (7.21)$$

$$\phi(x) = \phi(+\infty) + \frac{q}{16\pi\epsilon_0 x} \quad (7.22)$$

Ohmic contact transparency coefficient ($E_{00} = q \frac{\hbar\sqrt{N_d}}{2\sqrt{m^*\epsilon_{si}}}$)

$$T = e^{-2\sqrt{\frac{2m^*}{\hbar^2}} \sqrt{\frac{q^2 N_d}{2\epsilon_{si}} \frac{2\epsilon_{si}}{q N_d} (\phi_{bi} - V)}} = e^{-q \frac{(\phi_{bi} - V)}{E_{00}}} \quad (7.23)$$

Contact resistivity

$$\rho_c = \left(\frac{\partial J}{\partial V}\right)^{-1}|_{V=0} = \frac{E_{00}}{q} e^{q\phi_{bi}/E_{00}} \quad (7.24)$$

7.4 MOS capacitor

$$V_g - V_{fb} = V_s - \frac{Q_s}{C_{ox}} \quad (7.25)$$

Charge in the substrate

$$Q_s = \pm \sqrt{2kTN_a\epsilon_{si}} \left(e^{-qV_s/kT} + \frac{qV_s}{kT} - 1 + \frac{n_i^2}{N_a^2} \left(e^{qV_s/kT} - \frac{qV_s}{kT} - 1 \right) \right)^{1/2} \quad (7.26)$$