

Report Assignment 4: Control of a pendulum

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1 Modeling and Identification of the System

1.1 Theoretical continuous Model

The configuration of the pendulum placed on the cart is depicted in Figure 1, along with the definition of the position of the cart x and the angle of the pendulum θ . In Figure 2, the free body diagram of the pendulum is shown. The pendulum is depicted as a mass m , placed in the center of gravity of the the real pendulum. This mass is connected to the rotation point via a massless bar with length L . This way, the moment of inertia J can easily be computed:

$$J = m \cdot L^2 \quad (1)$$

To derive the continuous model of the velocity-steered cart with pendulum, Newton's second law of motion for rotation is used. There are three contributions to the total moment working on the pendulum system. These are caused by gravity, damping and an inertial force because the pendulum is placed in an accelerating reference frame. These can be filled in into Newton's second law:

$$J\ddot{\theta} = -mgL \sin(\theta) - m\ddot{x}L \cos(\theta) - c\dot{\theta} \quad (2)$$

Using Equation 1, this can be simplified to:

$$L\ddot{\theta} + \ddot{x} \cos(\theta) = -g \sin(\theta) - \frac{c}{mL} \dot{\theta} \quad (3)$$

The parameters of the theoretical continuous model of the velocity-steered cart are x and θ . The input is the cart velocity \dot{x} which has units $[m/s]$. The outputs of the model are the cart position x with units $[m]$ and the pendulum angle θ with units $[rad]$.

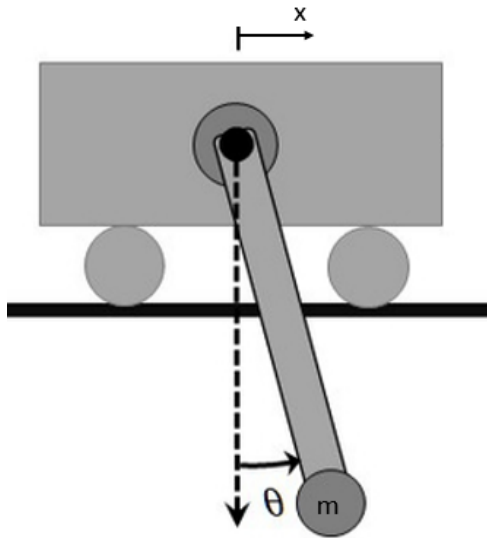


Figure 1: Depiction of the pendulum placed on the cart [3]

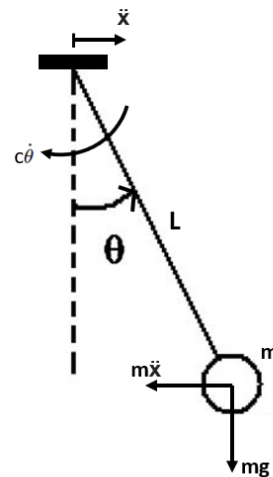


Figure 2: Free body diagram of the pendulum [1]

1.2 State-space Equation for the non-linear Model

To derive a state-space equation for the non-linear model, following states are used:

$$\xi = [x, \theta, L\dot{\theta} + \dot{x} \cos(\theta)]^T \quad (4)$$

In this state vector, x stands for the position of the cart and θ stands for the pendulum angle. In the third state $L\dot{\theta} + \dot{x} \cos(\theta)$, the tangential velocity of the centre of gravity of the pendulum with relation

to a standstill reference frame can be recognized. For this reason, we will call the third state v_{tan} from now on. The state vector then becomes:

$$\xi = [x, \theta, v_{tan}]^T \quad (5)$$

Using Equation 3 and the definition of ξ , the nonlinear state-space equation can be derived. The input is the velocity of the cart and is denoted as v_c .

$$\dot{\xi} = \mathbf{f}(\xi, v_c) = \begin{bmatrix} \dot{x} \\ \dot{\theta} \\ L\ddot{\theta} + \ddot{x} \cos(\theta) - \dot{x} \sin(\theta)\dot{\theta} \end{bmatrix} = \begin{bmatrix} v_c \\ \frac{v_{tan} - v_c \cos(\theta)}{L} \\ -g \sin(\theta) - \left(\frac{c}{mL} + v_c \sin(\theta)\right) \left(\frac{v_{tan} - v_c \cos(\theta)}{L}\right) \end{bmatrix} \quad (6)$$

$$\mathbf{y} = \begin{bmatrix} x \\ \theta \end{bmatrix} = \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 & 0 \end{bmatrix} \xi + 0 \cdot v_c \quad (7)$$

1.3 Linearization of the Model

The nonlinear model can be linearized around the equilibrium state $\xi_0 = [0, 0, 0]^T$. Both θ and v_{tan} have to be zero in the equilibrium state. The value of x doesn't really matter, but is taken equal to zero for convenience. The equilibrium input v_{c0} is also chosen to be equal to zero. Calculating the jacobian matrices \mathbf{F} and \mathbf{G} , we can rewrite the model as:

$$\delta \dot{\xi} = \mathbf{F} \delta \xi + \mathbf{G} \delta v_c \quad (8)$$

Where $\delta \xi$ and δv_c are defined as follows:

$$\begin{aligned} \delta \xi &= \xi - \xi_0 = \xi \\ \delta v_c &= v_c - v_{c0} = v_c \end{aligned} \quad (9)$$

Using nonlinear Equation 6, \mathbf{F} and \mathbf{G} are defined as:

$$\begin{aligned} \mathbf{F} &= \left. \frac{\partial \mathbf{f}}{\partial \xi} \right|_{\xi_0, v_{c0}} \\ \mathbf{G} &= \left. \frac{\partial \mathbf{f}}{\partial v_c} \right|_{\xi_0, v_{c0}} \end{aligned} \quad (10)$$

From Equation 10, the following matrices arise:

$$\begin{aligned} \mathbf{F} &= \begin{bmatrix} 0 & 0 & 0 \\ 0 & 0 & \frac{1}{L} \\ 0 & -g & \frac{-c}{mL^2} \end{bmatrix} \\ \mathbf{G} &= \begin{bmatrix} 1 \\ \frac{-1}{L} \\ \frac{c}{mL^2} \end{bmatrix} \end{aligned} \quad (11)$$

As the measurement equation was already linear, we find the following linear state-space model:

$$\delta \dot{\xi} = \begin{bmatrix} 0 & 0 & 0 \\ 0 & 0 & \frac{1}{L} \\ 0 & -g & \frac{-c}{mL^2} \end{bmatrix} \delta \xi + \begin{bmatrix} 1 \\ \frac{-1}{L} \\ \frac{c}{mL^2} \end{bmatrix} \delta v_c \quad (12)$$

$$\mathbf{y} = \begin{bmatrix} x \\ \theta \end{bmatrix} = \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 & 0 \end{bmatrix} \xi + 0 \cdot v_c \quad (13)$$

By applying the laplace transformation to Equation 12, following transfer functions can be found.

$$\begin{aligned} \frac{d\delta x}{dt} &= v_c \rightarrow H_x(s) = \frac{\delta X(s)}{\delta V_c(s)} = \frac{1}{s} \\ \frac{d\delta \theta}{dt} &= \frac{v_{tan} - v_c}{L} \rightarrow H_\theta(s) = \frac{\delta \Theta(s)}{\delta V_c(s)} = \frac{-1}{sL} \\ \frac{d\delta v_{tan}}{dt} &= -g\delta \theta - \frac{c}{mL^2}\delta v_{tan} + \frac{c}{mL^2}\delta v_c \rightarrow H_{v_{tan}}(s) = \frac{\delta V_{tan}(s)}{\delta V_c(s)} = \frac{1}{\frac{mL^2}{c}s + 1} \end{aligned} \quad (14)$$

1.4 Determination of the Pendulum Length

The damping ratio ζ can be determined, using the logarithmic decrement. In this experiment, the maximal amplitude of the angle θ for two consecutive periods are measured. This is shown in Figure 3, where T stands for the period of the oscillation. The logarithmic decrement δ is then defined as [2]:

$$\delta = \ln\left(\frac{\theta(t)}{\theta(t+T)}\right) = \frac{2\pi\zeta}{\sqrt{1-\zeta^2}} \quad (15)$$

Where $\theta(t)$ and $\theta(t+T)$ are both the values of the maximal angle in their period. From Equation 15, ζ can be derived:

$$\zeta = \frac{\delta}{\sqrt{(2\pi)^2 + \delta^2}} \quad (16)$$

By measuring the period of the oscillations, the distance L from the rotating point to the centre of gravity can be calculated. Since the pendulum has two bolts detached at the end of it, the centre of gravity will be located close to the end, but the distributed mass of the pendulum will cause the calculated length L to be smaller than the measured length from the rotating point to the end of the pendulum L_m .

From the measured period, we can derive the measured (damped) pulsation, which is an estimate for the real pulsation.

$$\omega_d = \frac{2\pi}{T} = \omega_n \sqrt{1-\zeta^2} \quad (17)$$

From Equation 17, the natural pulsation ω_n can be derived. As $\omega_n = \sqrt{\frac{g}{L}}$, L can be found as:

$$L = \frac{g}{\omega_n^2} = \frac{g(1-\zeta^2)}{\omega_d^2} \quad (18)$$

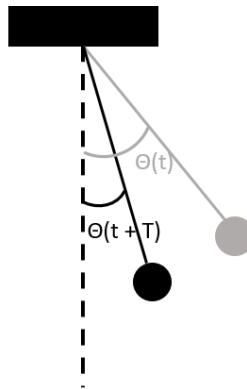


Figure 3: Measured values for the experiment to determine ζ

The numerical values are: $T = 0.71s$, $L = 0.1258m$, $\zeta = 0.0327[-]$. As expected, the measured length $L_m = 0.151m$ is larger than the calculated length L . If the damping is neglected, the measured pulsation ω_d is equal to the natural pulsation ω_n and the length can be calculated as $L' = \frac{g}{\omega_d^2} = 0.1259m$.

The damping coefficient c is related to the damping ratio ζ via Equation 19. As the pendulum mass is unknown, the moment of inertia J is unknown and c can not be calculated.

$$\zeta = \frac{c}{c_{crit}} = \frac{c}{2J\omega_n} \quad (19)$$

Important note: For the remainder of this report, the damping will be neglected.

1.5 Discretization

Linear model

To discretize the linear model, the forward Euler method is used:

$$\delta \dot{\xi} = \frac{\delta \xi[k+1] - \delta \xi[k]}{T_s} \quad (20)$$

Filling in Equation 20 in Equation 8 yields the following equation:

$$\delta \xi[k+1] = (\mathbf{I} + T_s \mathbf{F}) \delta \xi[k] + T_s \mathbf{G} \delta v_c[k] \quad (21)$$

Which can be translated into the following discretized, linear state-space model (where the damping is neglected, $c = 0$):

$$\begin{aligned} \delta \xi[k+1] &= \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 & \frac{T_s}{L} \\ 0 & -gT_s & 1 \end{bmatrix} \delta \xi[k] + \begin{bmatrix} T_s \\ -\frac{T_s}{L} \\ 0 \end{bmatrix} v_c[k] \\ \begin{bmatrix} x[k] \\ \theta[k] \end{bmatrix} &= \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 & 0 \end{bmatrix} \xi[k] + 0 \cdot v_c[k] \end{aligned} \quad (22)$$

Non-linear model

To discretize the non-linear model, the forward Euler method is used as well:

$$\dot{\xi} = \frac{\xi[k+1] - \xi[k]}{T_s} \quad (23)$$

By filling in Equation 23 in Equation 6 the following equation can be derived:

$$\xi[k+1] = T_s \mathbf{f}(\xi[k], v_c[k]) + \xi[k] \quad (24)$$

By neglecting the damping of the system, following discretized, nonlinear state-space model can be found:

$$\xi[k+1] = \begin{bmatrix} T_s \cdot \frac{v_{tan}[k] - v_c[k] \cos(\theta[k])}{L} + \theta[k] \\ T_s \left(-g \sin(\theta[k]) - v_c[k] \sin(\theta[k]) \frac{v_{tan}[k] - v_c[k] \cos(\theta[k])}{L} \right) + v_{tan}[k] \end{bmatrix} \quad (25)$$

$$\begin{bmatrix} x[k] \\ \theta[k] \end{bmatrix} = \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 & 0 \end{bmatrix} \xi[k] + 0 \cdot v_c[k] \quad (26)$$

2 Design and implementation of a linear Kalman filter

The linearized measurement equation is given by Equation 26. For the matrices Q , R and $\hat{P}_{0|0}$, the following numerical values are used:

$$\mathbf{R} = \begin{bmatrix} 2.7878 \cdot 10^{-9} & 0 \\ 0 & 9.4124 \cdot 10^{-6} \end{bmatrix} \begin{bmatrix} \text{m}^2 \\ \text{rad}^2 \end{bmatrix} \quad (27)$$

$$\mathbf{Q} = \begin{bmatrix} 2.7878 \cdot 10^{-8} & 0 & 0 \\ 0 & 9.4124 \cdot 10^{-8} & 0 \\ 0 & 0 & 10^{-4} \end{bmatrix} \begin{bmatrix} \text{m}^2 \\ \text{rad}^2 \\ \left(\frac{\text{m}}{\text{s}}\right)^2 \end{bmatrix} \quad (28)$$

$$\hat{\mathbf{P}}_{0|0} = 0 \quad (29)$$

3 Design and implementation of an extended Kalman filter

3.1 Nonlinear measurement equation

As is already written down in the nonlinear state-space model Equations 7, the measurement equation based on the nonlinear system equations is actually a linear equation. This is caused by the fact that the two outputs x and θ are two states. The measurement equation based on the nonlinear system equations can be written as:

$$\mathbf{y} = \begin{bmatrix} x \\ \theta \end{bmatrix} = \mathbf{g}(\xi, v_c) = \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 & 0 \end{bmatrix} \xi + 0 \cdot v_c \quad (30)$$

3.2 Jacobian of the state and measurement equation

The Jacobian matrix of the state equation and the Jacobian matrix of the measurement equation can be found by taking the derivative of the functions \mathbf{f} (Equation 25) and \mathbf{g} (Equation 30) to the state vector ξ

$$\begin{aligned} \mathbf{A} &= \frac{\partial \mathbf{f}}{\partial \xi} \\ \mathbf{C} &= \frac{\partial \mathbf{g}}{\partial \xi} \end{aligned} \quad (31)$$

Unlike the linear Kalman filter, the extended Kalman filter uses discretized jacobian matrices evaluated in the current state estimate and not in the equilibrium state. Using Equations 31, following expressions can be derived for the discrete time jacobians, starting from nonlinear, discrete state-space model 25. Damping is neglected:

$$\begin{aligned} \mathbf{A} &= \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 + T_s \frac{v_c \sin(\theta)}{L} & \frac{T_s}{L} \\ 0 & T_s \left(-g \cos(\theta) - \frac{v_{tan} - v_c \cos(\theta)}{L} \cdot v_c \cos(\theta) - \frac{(v_c \sin(\theta))^2}{L} \right) & 1 + T_s \frac{-v_c \sin(\theta)}{L} \end{bmatrix} \\ \mathbf{C} &= \begin{bmatrix} 1 & 0 & 0 \\ 0 & 1 & 0 \end{bmatrix} \end{aligned} \quad (32)$$

3.3 Implementation of the extended Kalman filter

Since the linearization of the model has no influence on the measurement noise covariance or the covariance of the initial state estimation errors, the values for \mathbf{R} and $\hat{\mathbf{P}}_{0|0}$ for the extended Kalman filter are taken equal to those used in the linear Kalman filter (see Equations [VERWIJZEN NAAR VROEGERE MATRICES](#)). As the nonlinear model is used for the extended Kalman filter, the model should be more precise and thus the proces noise should be lower. For this reason \mathbf{Q} is taken one order of magnitude smaller than the \mathbf{Q} used in the linear Kalman filter.

$$\mathbf{Q} = \begin{bmatrix} 2.7878 \cdot 10^{-9} & 0 & 0 \\ 0 & 2.3511 \cdot 10^{-9} & 0 \\ 0 & 0 & 10^{-5} \end{bmatrix} \quad (33)$$

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4 Design and implementation of a state feedback controller based on the linearized model

4.1 Design of a linear quadratic regulator

The objective of the LQR is to find the control input $v_c[k]$ that moves the system states $\xi \neq 0$ to $\mathbf{0}$, in a way the performance criterion \mathcal{J} is minimized. This means a tradeoff has to be made between

performane \mathcal{J}_p , the speed with which the states go to zero (or a desired state), and the controll effort \mathcal{J}_c . The criterion is given in Equation 34.

$$\mathcal{J} = \mathcal{J}_p + \mathcal{J}_c = \sum_{k=0}^{\infty} \xi[k]^T \mathbf{Q} \xi[k] + v_c[k] R v_c[k] \quad (34)$$

The matrix \mathbf{Q} and the value R are design parameters. These values determine which part of the tradeoff is most important in this particular design: performance or control effort. The tuning of the parameters and thus the design of the LQR itself is done in Section 4.3.

4.2 Design of a feedforward gain

The blockdiagram of the system with feedforward compensation can be found in Figure 4.

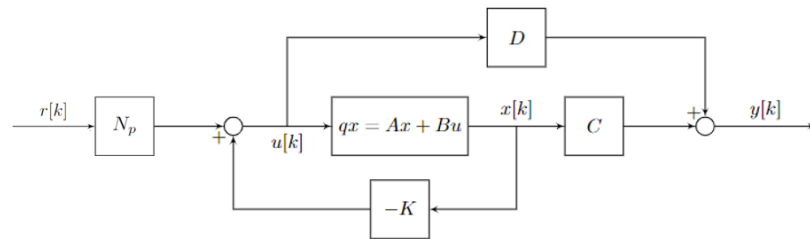


Figure 4: Blockdiagram of the system with feedforward compensation

The feedforward gain N_p is calculated such that the steady-state error equals zero for a step reference in desired position, which is denoted with $r[k]$. The pendulum mass position can be written as:

$$x_p = x + L \cdot \sin(\theta) = x + L \cdot \theta \quad (35)$$

x_p is thus a linear combination of the two outputs of the linear system. The total transfer function $\mathbf{H}(z)$ of the system is thus a vector containing 2 transfer functions: $H_x(z) = \frac{X(z)}{V_c(z)}$ and $\frac{\Theta(z)}{V_c(z)}$. The pendulum mass position can be calculated starting from a given v_c as follows:

$$X_p(z) = (H_x(z) + LH_\theta(z))V_c(z) \quad (36)$$

Following the reasoning on C9, slide 54 of the slides of the course Control Theory [4], the expression for N_p to

4.3 Implementation of the controller

References

- [1] Aurelio Arenas. The use of a nintendo wii remote control in physics experiments. https://www.researchgate.net/publication/258272199_The_use_of_a_Nintendo_Wii_remote_control_in_physics_experiments, 2013. Accessed December 17th 2021.
- [2] W. Desmet. *Mechanische trillingen - Slides*. Cursusdienst VTK, 2021.
- [3] Michel Levis. Common and not so common pendulum configurations. <https://www.quanser.com/blog/common-and-not-so-common-pendulum-configurations/>, 2019. Accessed December 17th 2021.
- [4] Swevers J. Pipeleers G. *Control Theory - Handouts*. Cursusdienst VTK, 2021.