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An Automated Triple Modular Redundancy EDA Flow for Yosys

by

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Prof. Michael Brünig,
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Dear Professor Brünig,

In accordance with the requirements of the Degree of Bachelor of Computer Science (Honours) in the School of Electrical Engineering and Computer Science, I submit the following thesis entitled

“An Automated Triple Modular Redundancy EDA Flow for Yosys”

The thesis was performed under the supervision of Associate Professor John Williams. I declare that the work submitted in the thesis is my own, except as acknowledged in the text and footnotes, and that it has not previously been submitted for a degree at the University of Queensland or any other institution.

Yours sincerely,

Matthew Lawrence Young

cosmic rays n.

Notionally, the cause of bit rot. However, this is a semi-independent usage that may be invoked as a humorous way to handwave away any minor randomness that doesn't seem worth the bother of investigating. "Hey, Eric – I just got a burst of garbage on my tube, where did that come from?" "Cosmic rays, I guess."

Compare **sunspots**, **phase of the moon**.

— *The New Hacker's Dictionary*, 1991

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Abstract

Safety-critical sectors require Application Specific Integrated Circuit (ASIC) designs and Field Programmable Gate Array (FPGA) gateware to be fault-tolerant. In particular, high-reliability computer systems used in spaceflight computing need to mitigate the effects of Single Event Upsets (SEUs) caused by ionising radiation. One common fault-tolerant design technique is Triple Modular Redundancy (TMR), which mitigates SEUs by triplicating key parts of the design and using voter circuits. Typically, this is manually implemented by designers at the Hardware Description Language (HDL) level, but this is error-prone and time-consuming. Leveraging the power and flexibility of the open-source Yosys Electronic Design Automation (EDA) tool, in this thesis, I present *TaMaRa*: a novel fully automated TMR flow, implemented as a Yosys plugin. I describe the design and implementation of the TaMaRa tool, and present extensive test results using a combination of manual tests, formal verification and RTL fuzzing techniques.

Contents

Acknowledgements	iv
Abstract	v
Contents	vi
List of Figures	viii
List of Abbreviations and Symbols	ix
1. Introduction	1
1.1. Yosys internals	3
2. Literature review	5
2.1. Introduction, methodology and terminology	5
2.2. Fault tolerant computing and redundancy	5
2.3. Netlist-level approaches	7
2.4. Design-level approaches	11
2.5. TMR verification	12
2.6. Formal verification	13
2.7. RTL fuzzing	14
3. Methodology	16
3.1. Concept	16
3.2. Implementation	17
3.2.1. Voter design	18
3.2.2. RTLIL netlist analysis	21
3.2.3. Backwards breadth-first search	21
3.2.4. Combinatorial replication	22
3.2.5. Voter insertion	22
3.2.6. Wiring	23
3.2.7. Wiring fix-up	24
3.2.8. Search continuation	25
3.2.9. Summary	25
3.3. Verification	26
3.3.1. Manual verification	27
3.3.2. Formal verification	27
3.3.3. RTL fuzzing techniques	28
4. Results	29
4.1. Testbench suite	29
4.1.1. Combinatorial circuits	29
4.1.2. Multi-bit combinatorial circuits	30
4.1.3. Sequential circuits	31

4.1.4. Multi-cone circuits	31
4.1.5. Feedback circuits	32
4.2. Formal verification	33
4.2.1. Equivalence checking	33
4.2.2. Fault injection	33
4.2.3. Fault injection studies: Protected voter	33
4.2.4. Fault injection studies: Unprotected voter	36
4.2.5. Analysis of fault injection results	39
4.3. RTL fuzzing	40
5. Conclusion	41
5.1. Future work	41
Appendix A Source code	42
Bibliography	43

List of Figures

Figure 1	Diagram demonstrating how TMR is inserted into an abstract design	2
Figure 2	Simplified representation of a typical EDA synthesis flow	2
Figure 3	Class diagram of the TaMaRa codebase	18
Figure 4	Logisim Evolution schematic for voter circuit	19
Figure 5	Voter schematic generated by Yosys	20
Figure 6	Demonstration of RTLILWireConnections construction	21
Figure 7	Description of TaMaRa’s definition of logic cones	22
Figure 8	Schematic of circuit before running the multi-driver fixer	24
Figure 9	Schematic of circuit after running the multi-driver fixer	24
Figure 10	Demonstration of search continuation for two circuits	25
Figure 11	Logic flow of the TaMaRa TMR algorithm	26
Figure 12	Unmitigated vs. protected voter for the mux_2bit circuit	39
Table 1	Truth table for a single-bit majority voter	19
Table 2	Table of single-bit combinatorial circuit designs	29
Table 3	Table of multi-bit combinatorial circuit designs	30
Table 4	Table of sequential circuit designs	31
Table 5	Table of multi-cone circuits	31
Table 6	Table of feedback circuits	32
Table 7	Protected voter fault injection study results	34
Table 8	Unprotected voter fault injection study results	36
Table 9	Voter area for different circuits	39
Listing 1	Usage of the (* tamara_error_sink *) annotation	17
Listing 2	Partial listing of C++ macros to generate voter	20
Listing 3	SystemVerilog implementation of 1-bit majority voter	21
Listing 4	Yosys script to deselect TaMaRa voter wires/cells	33

List of Abbreviations and Symbols

Abbreviation	Meaning
ASIC	Application Specific Integrated Circuit
BFS	Breadth-First Search
CI	Continuous Integration
CMOS	Complementary Metal-Oxide Semiconductor
COTS	Commercial Off The Shelf
DFF	D-Flip-Flop
EDA	Electronic Design Automation
FD-SOI	Fully Depleted Silicon-on-Insulator
FF	D-Flip-Flop
FPGA	Field Programmable Gate Array
HDL	Hardware Description Language
IC	Integrated Circuit
LUT	Lookup Table
P&R / PnR	Place and Route
PDK	Process Design Kit
PLL	Phase Locked Loop
PPA	Power, Performance and Area
RTL	Register Transfer Level
RTLIL	RTL Intermediate Language

Abbreviation	Meaning
SEU	Single Event Upset
SRAM	Static Random Access Memory
TMR	Triple Modular Redundancy

Chapter 1

Introduction

For safety-critical sectors such as aerospace, defence, and medicine, both Application Specific Integrated Circuits (ASICs) and Field Programmable Gate Array (FPGA) gateware must be designed to be fault tolerant to prevent catastrophic malfunctions. In the context of digital electronics, *fault tolerant* means that the design is able to gracefully recover and continue operating in the event of a fault, or upset. A Single Event Upset (SEU) occurs when ionising radiation strikes a transistor on a digital circuit, causing it to transition from a 1 to a 0, or vice versa. This type of upset is most common in space, where the Earth's magnetosphere is not present to dissipate the ionising particles [1]. On an unprotected system, an unlucky SEU may corrupt the system's state to such a severe degree that it may cause destruction or loss of life - particularly important given the safety-critical nature of most space-fairing systems (satellites, crew capsules, missiles, etc). Thus, fault tolerant computing is widely studied and applied for space-based computing systems.

One common fault-tolerant design technique is Triple Modular Redundancy (TMR), which mitigates SEUs by triplicating key parts of the design and using voter circuits to select a non-corrupted result if an SEU occurs (see [Figure 1](#)). Typically, TMR is manually designed at the Hardware Description Language (HDL) level, for example, by manually instantiating three copies of the target module, designing a voter circuit, and linking them all together. However, this approach is an additional time-consuming and potentially error-prone step in the already complex design pipeline.



Figure 1: Diagram demonstrating how TMR is inserted into an abstract design

Modern digital ICs and FPGAs are described using Hardware Description Languages (HDLs), such as SystemVerilog or VHDL. The process of transforming this high level description into a photolithography mask (for ICs) or bitstream (for FPGAs) is achieved through the use of Electronic Design Automation (EDA) tools. This generally comprises of the following stages (Figure 2):



Figure 2: Simplified representation of a typical EDA synthesis flow

- **Synthesis:** The transformation of a high-level textual HDL description into a lower level synthesisable netlist.
 - **Elaboration:** Includes the instantiation of HDL modules, resolution of generic parameters and constants. Like compilers, synthesis tools are typically split into frontend/backend, and elaboration could be considered a frontend/language parsing task.

- ▶ **Optimisation:** This includes a multitude of tasks, anywhere from small peep-hole optimisations, to completely re-coding FSMs. In commercial tools, this is typically timing driven.
- ▶ **Technology mapping:** This involves mapping the technology-independent netlist to the target platform, whether that be FPGA LUTs, or ASIC standard cells.
- **Placement:** The process of optimally placing the netlist onto the target device. For FPGAs, this involves choosing which logic elements to use. For digital ICs, this is much more complex and manual - usually done by dedicated layout engineers who design a *floorplan*.
- **Routing:** The process of optimally connecting all the placed logic elements (FPGAs) or standard cells (ICs).

Due to their enormous complexity and cutting-edge nature, most IC EDA tools are commercial proprietary software sold by the big three vendors: Synopsys, Cadence and Siemens. These are economically infeasible for almost all researchers, and even if they could be licenced, would not be possible to extend to implement custom synthesis passes. The major FPGA vendors, AMD and Intel, also develop their own EDA tools for each of their own devices, which are often cheaper or free. However, these tools are still proprietary software and cannot be modified by researchers. Until recently, there was no freely available, research-grade, open-source EDA tool available for study and improvement. That changed with the introduction of Yosys [2]. Yosys is a capable synthesis tool that can emit optimised netlists for various FPGA families as well as a few silicon process nodes (e.g. Skywater 130nm). When combined with the Nextpnr place and route tool [3], Yosys+Nextpnr forms a fully end-to-end FPGA synthesis flow for Lattice iCE40 and ECP5 devices. Importantly, for this thesis, Yosys can be modified either by changing the source code or by developing modular plugins that can be dynamically loaded at runtime.

This thesis will focus on the design and implementation of *TaMaRa*, an automated Triple Modular Redundancy EDA flow for Yosys. In [Chapter 2](#), I present a comprehensive literature review of prior TMR algorithms by classifying them into dichotomy of either netlist-level or design-level approaches. I evaluate the strengths and weakness of each approach, and determine how it will shape the *TaMaRa* algorithm. In [Chapter 3](#), I introduce the *TaMaRa* algorithm, and demonstrate how it was implemented as a Yosys plugin. Finally, in [Chapter 4](#), I show the results of the *TaMaRa* algorithm for a number of real-world circuits and measure its ability to mitigate SEUs.

1.1. Yosys internals

Yosys supports dynamically loading plugins at runtime. These plugins are compiled against the Yosys codebase, and are compiled into Unix shared objects (.so files). This allows users to define and register custom passes and frontends within the main Yosys application, without having to trouble the upstream maintainers with the maintenance of new code. This is precisely why the Yosys authors advised *TaMaRa* to be implemented

as a Yosys plugin, rather than as an upstream contribution [4]. This plugin system is a unique and powerful part of Yosys, and one of the main advantages of the tool being open-source. End users are free to design and implement their own plugins, under their own choice of licence, to extend Yosys in any way they see fit. Comparatively, proprietary tools are limited to rather simple Tcl scripting, as further modification is locked away behind complex intellectual property (IP) rights, including patents, and non-disclosure agreements (NDAs).

Yosys uses *frontends* to read various Register Transfer Languages (RTLs), such as Verilog or SystemVerilog. Using the typical combination of a lexer and parser, Yosys transforms RTL source code into an Abstract Syntax Tree (AST), and then into an intermediate language called RTL Intermediate Language (RTLIL). RTLIL is, in essence, a model of a given circuit's netlist at various different levels of abstraction. RTLIL can be used anywhere from a near direct 1:1 mapping with the original RTL, complete with processes and annotations, all the way down to very low-level FPGA/ASIC specific primitives. The typical Yosys flow is to use its extensive set of built-in commands and synthesis scripts to process a circuit from this high-level abstraction, down to device-specific low-level primitives; for example, ASIC standard cells for a given process node. This is virtually identical to the flow used by commercial tools such as Synopsys' Design Compiler or Xilinx's Vivado.

TaMaRa operates at the netlist level, which in the context of Yosys means operating on RTLIL circuits. Internally, RTLIL is implemented as a set of C++ classes that describe the general structure of a netlist as wires (`RTLIL::Wire`) and cells (`RTLIL::Cell`). Wires may potentially be multi-bit, which introduces a challenge as TaMaRa voters are single-bit. Groups of wires and cells can be bundled into a module (`RTLIL::Module`). Modules are arranged in a tree structure, where the root of the tree is known as the top module. RTLIL is one of the most important and powerful parts of Yosys, because it allows plugins like TaMaRa to operate on a common intermediate representation of a circuit netlist, irrespective of the user's choice of input RTL language and/or output type. This means that TaMaRa can operate exactly the same for a user using VHDL for a Lattice iCE40 FPGA, and a user using Verilog for a Skywater 130 nm ASIC. RTLIL's importance is further elaborated on by Wolf [2] and Shah et al. [3]. In essence, the unique combination of Yosys being open-source, its runtime plugin system, and its RTL Intermediate Language is what makes Yosys the ideal platform to develop the TaMaRa algorithm for.

Chapter 2

Literature review

2.1. Introduction, methodology and terminology

The automation of triple modular redundancy, as well as associated topics such as general fault-tolerant computing methods and the effects of SEUs on digital hardware, have been studied a fair amount in academic literature. Several authors have invented a number of approaches to automate TMR, at various levels of granularity, and at various points in the FPGA/ASIC synthesis pipeline. This presents an interesting challenge to systematically review and categorise. To address this, I propose that all automated TMR approaches can be fundamentally categorised into the following dichotomy:

- **Design-level approaches** (“thinking in terms of HDL”): These approaches treat the design as *modules*, and introduce TMR by replicating these modules. A module could be anything from an entire CPU, to a register file, to even a single combinatorial circuit or AND gate. Once the modules are replicated, voters are inserted.
- **Netlist-level approaches** (“thinking in terms of circuits”): These approaches treat the design as a *circuit* or *netlist*, which is internally represented as a graph. TMR is introduced using graph theory algorithms to *cut* the graph in a particular way and insert voters.

Using these two design paradigms as a guiding point, I analyse the literature on automated TMR, as well as background literature on fault-tolerant computing.

2.2. Fault tolerant computing and redundancy

The application of triple modular redundancy to computer systems was first introduced into academia by Lyons and Vanderkul [5] in 1962. Like much of computer science, however, the authors trace the original concept back to John von Neumann. In addition to introducing the application of TMR to computer systems, the authors also provide a rigorous Monte-Carlo mathematical analysis of the reliability of TMR. One important takeaway from this is that the only way to make a system reliably redundant is to split it into multiple components, each of which is more reliable than the system as a whole. In the modern FPGA concept, this implies applying TMR at an Register Transfer Level (RTL) module level, although as we will soon see, more optimal and finer grained TMR can be applied. Although their Monte Carlo analysis shows that TMR dramatically improves reliability, they importantly show that as the number of modules M in the computer system increases, the computer will eventually become less reliable. This is due to the fact that the voter circuits may not themselves be perfectly reliable, and is important to note for FPGA and ASIC designs which may instantiate hundreds or potentially thousands of modules.

Instead of triple modular redundancy, ASICs can be designed using rad-hardened CMOS process nodes or design techniques. Much has been written about rad-hardened microprocessors, of which many are deployed (and continue to be deployed) in space to this day. One such example is the RAD750 [6], a rad-hardened PowerPC CPU for space applications designed by Berger et al. of BAE Systems. They claim “5-6 orders of magnitude” better SEU performance compared to a stock PowerPC 750 under intense radiation conditions. The processor is manufactured on a six-layer commercial 250 nm process node, using specialty design considerations for the RAM, PLLs, and standard cell libraries. Despite using special design techniques, the process node itself is standard commercial CMOS node and is not inherently rad-hardened. The authors particularly draw attention to the development of a special SEU-hardened RAM cell, although unfortunately they do not elaborate on the exact implementation method used. However, they do mention that these techniques increase the die area from 67 mm² in a standard PowerPC 750, to 120 mm² in the RAD750, a ~1.7x increase. Berger et al. also used an extensive verification methodology, including the formal verification of the gate-level netlist and functional VHDL simulation. The RAD750 has been deployed on numerous high-profile missions including the James Webb Space Telescope and Curiosity Mars rover. Despite its wide utilisation, however, the RAD750 remains extremely expensive - costing over \$200,000 USD in 2021 [7]. This makes it well out of the reach of research groups, and possibly even difficult to acquire for space agencies like NASA.

In addition to commercial CMOS process nodes, there are also specialty rad-hardened process nodes designed by several fabs. One such example is Skywater Technologies’ 90 nm FD-SOI (“Fully Depleted Silicon-On-Insulator”) node. The FD-SOI process, in particular, has been shown to have inherent resistance to SEUs and ionising radiation due to its top thin silicon film and buried insulating oxide layer [8]. Despite this, unfortunately, FD-SOI is an advanced process node that is often expensive to manufacture.

Instead of the above, with a sufficiently reliable TMR technique (that this research ideally would like to help create), it should theoretically be possible to use a commercial-off-the-shelf (COTS) FPGA for mission critical space systems, reducing cost enormously - this is one of the key value propositions of automated TMR research. Of course, TMR is not flawless: its well-known limitations in power, performance and area (PPA) have been documented extensively in the literature, particularly by Johnson [9], [10]. Despite this, TMR does have the advantage of being more general purpose and cost-effective than a specially designed ASIC like the RAD750. TMR can be applied to any design, FPGA or ASIC, at various different levels of granularity and hierarchy, allowing for studies of different trade-offs. For ASICs in particular, unlike the RAD750, TMR as a design technique does not need to be specially ported to new process nodes: an automated TMR approach could be applied to a circuit on a 250 nm or 25 nm process node without any major design changes. Nonetheless, specialty rad-hardened ASICs will likely to see future use in space applications. In fact, it’s entirely possible that a rad-hardened FPGA *in combination* with an automated TMR technique is the best way of ensuring reliability.

2.3. Netlist-level approaches

Recognising that prior literature focused mostly around manual or theoretical TMR, and the limitations of a manual approach, Johnson and Wirthlin [9] introduced four algorithms for the automatic insertion of TMR voters in a circuit, with a particular focus on timing and area trade-offs. Together with the thesis this paper was based on [10], these two publications form the seminal works on automated TMR for digital EDA. Johnson’s algorithm operates on a post-synthesis netlist before technology mapping. First, he creates three copies of the original circuit, then triplicates component instantiations and wire nets, and finally connects the nets in such a way that the behaviour of the original circuit is preserved. This is described as the “easy part” of TMR - the more complex step is selecting both a valid *and* optimal placement for majority voters. Johnson identifies four main classes of voters. Note that in this section, “SRAM scrubbing” refers to Johnson’s method of dynamic runtime reconfiguration of the FPGA configuration SRAM to correct SEUs.

1. **Reducing voters:** Combines the output from three TMR replicas into a single output, in other words, a single majority voter. Used on circuit outputs.
2. **Partitioning voters:** Used to increase reliability within a circuit by partitioning it, and applying TMR separately to each partition. Johnson states that if only reducing voters were used in a circuit, errors would be masked from SRAM scrubbing as long as they only occur in one replica at a time. In addition, multiple SEUs in close proximity can prevent the TMR redundancy from working correctly. Partitioning voters have the benefit of dividing the circuit into independent partitions that can tolerate SEUs independently. One important takeaway that Johnson mentions is that there is an optimal balance between the number of partitions, which increases the likelihood of separate SEUs affecting multiple partitions, and having *too many* partitions which reduces reliability due to the voters being affected. This relates to the early research conducted by Lyons and Vanderkul [5].
3. **Clock domain crossing voters:** These are used due to the special considerations when TMR circuits cross multiple clock domains. In particular, metastability effects are a serious consideration for clock domain crossing voters. Johnson implements this type of voter using a small train of consecutive flip-flops to attempt to reduce the probability of metastable values propagating. However, for TaMaRa, due to the very tight time constraints of an Honours thesis, we will likely not consider multiple clock domains, and thus metastable voters will not be required.
4. **Synchronisation voters:** These are required when SRAM scrubbing is used with TMR that includes sequential logic (i.e. FFs, so most designs). These are meant to restore correct register state after FPGAs are repaired by SRAM scrubbing. Again due to time constraints and the vendor-specific nature of the process, TaMaRa will leave SRAM scrubbing up to the end user, using the provided error signal from the majority voters. Rather than supporting dynamic SRAM scrubbing (as in Bridford et al. [11]), we will suggest users simply reset the device when a fault is detected.

One other consideration that Johnson takes into account is illegal or undesirable voter cuts (a “voter cut” is his terminology for splicing a netlist and inserting a majority voter). He notes that some netlist cuts are illegal, for example, some Xilinx FPGAs do not support configurable routing between different types of primitives, particularly DSP primitives. He also very interestingly notes that there are undesirable, but not strictly illegal cuts that may be performed. These would, for example, break high speed carry chains on Xilinx devices and impact performance. This is a very interesting observation, as it implies the possibility of a placement/routing aware TMR algorithm. This is a fascinating topic for future research, but time does not permit its implementation in TaMaRa. Instead, TaMaRa will likely leave design legalisation to Nextpnr and not strictly consider performance when inserting voters. The majority of Johnson’s work, and the complexity he describes, concerns the insertion of synchronisation voters using graph theory algorithms such as Strongly Connected Components (SCC). For TaMaRa, we declared that we do not need synchronisation voters, as we do not perform dynamic SRAM scrubbing, instead fully rebooting the device if we detect a fault. This should mean that TaMaRa is a lot easier to implement. Nonetheless, however, I believe it may be possible to use some of Johnson’s SCC algorithm to elegantly decompose a netlist into partitions, and insert partition voters. We will most likely insert reducing voters and partitioning voters, and if time permits, clock domain crossing voters as well.

Whilst they provide an excellent design of TMR insertion algorithms, and a very thorough analysis of their area and timing trade-offs, Johnson and Wirthlin do not have a rigorous analysis of the correctness of these algorithms. They produce experimental results demonstrating the timing and area trade-offs of the TMR algorithms on a real Xilinx Virtix 1000 FPGA, up to the point of P&R, but do not run it on a real device. More importantly, they also do not have any formal verification or simulated SEU scenarios to prove that the algorithms both work as intended, and keep the underlying behaviour of the circuit the same. Finally, in his thesis [10], Johnson states that the benchmark designs were synthesised using a combination of the commercial Synopsys Synplify tool, and the *BYU-LANL Triple Modular Redundancy (BL-TMR) Tool*. This Java-based set of tools ingest EDIF-format netlists, perform TMR on them, and write the processed result to a new EDIF netlist, which can be re-ingested by the synthesis program for place and route. This is quite a complex process, and was also designed before Yosys was introduced in 2013. It would be better if the TMR pass was instead integrated directly into the synthesis tool - which is only possible for Yosys, as Synplify is commercial proprietary software. This is especially important for industry users who often have long and complicated synthesis flows.

Later, Skouson et al. [12] (from the same lab as above) introduced SpyDrNet, a Python-based netlist transformation tool that also implements TMR using the same algorithm as above. SpyDrNet is a great general purpose transformation tool for research purposes, but again is a separate tool that is not integrated *directly* into the synthesis process. I instead aim to make a *production* ready tool, with a focus on ease-of-use, correctness and performance.

Using a similar approach, Benites and Kastensmidt [13], and Benites’ thesis [14], introduce an automated TMR approach implemented as a Tcl script for use in Cadence tools. They distinguish between “coarse grained TMR” (which they call “CGTMR”), applied at the RTL module level, and “fine grained TMR” (which they call “FGTMR”), applied at the sub-module (i.e. net) level. Building on that, they develop an approach that replicates both combinatorial and sequential circuits, which they call “fine grain distributed TMR” or “FGDTMR”. They split their TMR pipeline into three stages: implementation (“TMRi”), optimisation (“TMRo”), and verification (“TMRv”). The implementation stage works by creating a new design to house the TMR design (which I’ll call the “container design”), and instantiating copies of the original circuit in the container design. Depending on which mode the user selects, the authors state that either each “sequential gate” will be replaced by three copies and a voter, or “triplicated voters” will be inserted. What happens in the optimisation stage is not clear as Benites does not elaborate at all, but he does state it’s only relevant for ASICs and involves “gate sizing”. For verification, Benites uses a combination of fault-injection simulation (where SEUs are intentionally injected into the simulation), and formal verification through equivalence checking. Equivalence checking involves the use of Boolean satisfiability solvers (“SAT solvers”) to mathematically prove one circuit is equivalent to another. Benites’ key verification contribution is identifying a more optimal way to use equivalence checking to verify fine-grained TMR. He identified that each combinatorial logic path will be composed of a path identical to the original logic, plus one or more voters. This way, he only has to prove that each “logic cone” as he describes it is equivalent to the original circuit. Later on, he also uses a more broad-phase equivalence checking system to prove that the circuits pre and post-TMR have the same behaviours.

One of the most important takeaways from these works are related to clock synchronisation. Benites interestingly chooses to not replicate clocks or asynchronous reset lines, which he states is due to clock skew and challenges with multiple clock domains created by the redundancy. Due to the clear challenges involved, ignoring clocks and asynchronous resets is a reasonable limitation introduced by the authors, and potentially reasonable for us to introduce as well. Nonetheless, it is a limitation I would like to address in TaMaRa if possible, since leaving these elements unprotected creates a serious hole that would likely preclude its real-world usage¹. Arguably, the most important takeaway from Benites’ work is the use of equivalence checking in the TMR verification stage. This is especially important since Johnson [9] did not formally verify his approach. Benites’ usage of formal verification, in particular, equivalence checking, is an excellent starting point to design the verification methodology for TaMaRa.

Xilinx, the largest designer of FPGAs, also has a netlist-level TMR software package known as TMRTool [15]. This implements a Xilinx proprietary algorithm known as

¹My view is essentially that an unprotected circuit remains unprotected, regardless of how difficult it is to correct clock skewing. In other words, simply saying that the clock skew exists doesn’t magically resolve the issue. In Honours, we are severely time limited, but it’s still my goal to address this limitation if possible.

XTMR, which differs from traditional TMR approaches in that it also aims to correct faults introduced into the circuit by SEUs (rather than just masking their existence). Xilinx also aims to address single-event transients (“SETs”), where ionising radiation causes voltage spikes on the FPGA routing fabric. TMRTTool follows a similar approach to the other netlist-level algorithms described above, with some small improvements and Xilinx-specific features. The flow first triplicates all inputs, combinatorial logic and routing. Then, it inserts voters downstream in the circuit, particularly on finite state machine (FSM) feedback paths. One important difference is that, at this point in the flow, Xilinx also decides to triplicate the voters themselves. This means there is no single point of failure (which improves redundancy), although it has a higher area cost than approaches that do not triplicate voters. In addition, TMRTTool is designed to be used with configuration scrubbing. Xilinx has much further research on FPGA configuration scrubbing [11]. The two main approaches are either a full reboot, or a partial runtime reconfiguration. Since the FPGA configuration is stored in an SRAM that’s read at boot-up, a full reboot will naturally reconfigure the device, and thus correct any logic/routing issues caused by SEUs. However, a more efficient solution is only re-flashing the sectors of the FPGA that are known to be affected by SEUs. This is known as partial runtime reconfiguration. Unfortunately, as noted in the Xilinx documentation, this partial reconfiguration is a vendor-specific process. It would not be possible to design a multi-vendor runtime reconfiguration approach, and worse still, much of this specification is still undocumented and proprietary, precluding its integration with Yosys or Nextpnr. Despite this, we could provide end-users with an error signal from the majority voter, which could be used to one form of reconfiguration if desired. The two most relevant components of TMRTTool to the TaMaRa algorithm are its consideration of feedback paths for FSMs, and its consideration of redundant clock domains. Both of these considerations are mentioned in the other netlist-level approaches, but it seems to occupy a considerable amount of engineering time and effort for Xilinx, and thus can be expected to be a significant issue for TaMaRa as well. TMRTTool’s FSM feedback is important to ensure the synchronisation of triplicated redundant FSMs, but unfortunately requires manual verification in some cases to ensure Xilinx’s synthesis has not introduced problems to the design. Finally, TMRTTool also has a very flexible architecture. The implementation strategy can be customised to various different approaches. Most are Xilinx-specific, but two relevant ones to TaMaRa are “Standard” and “Don’t Touch”. “Standard” works by triplicating the underlying FPGA primitives and inserting voters, as usual. “Don’t Touch”, however, is important to be added to FPGA primitives that cannot be replicated, and avoids TMR entirely. This would be very beneficial to add as an option to the TaMaRa algorithm.

On the lower level side, Hindman et al. [16] introduce an ASIC standard-cell based automated TMR approach. When digital circuits are synthesised into ASICs, they are technology mapped onto standard cells provided by the foundry as part of their Process Design Kit (PDK). For example, SkyWater Technology provides an open-source 130 nm ASIC PDK, which contains standard cells for NAND gates, muxes and more [17]. The

authors design a TMR flip-flop cell, known as a “Triple Redundant Self Correcting Master-Slave Flip-Flop” (TRSCMSFF), that mitigates SEUs at the implementation level. Since this is so low level and operates below the entire synthesis/place and route pipeline, their approach has the advantage that *any* design - including proprietary encrypted IP cores that are (unfortunately) common in industry - can be made redundant. Very importantly, the original design need not be aware of the TMR implementation, so this approach fulfills my goal of making TMR available seamlessly to designers. The authors demonstrate that the TRSCMSFF cell adds minimal overhead to logic speed and power consumption, and even perform a real-life radiation test under a high energy ion beam. Overall, this is an excellent approach for ASICs. However, this approach, being standard-cell specific, cannot be applied to FPGA designs. Rather, the FPGA manufacturers themselves would need to apply this method to make a series of specially rad-hardened devices. It would also appear that designers would have to port the TRSCMSFF cell to each fab and process node they intend to target. While TaMaRa will have worse power, performance and area (PPA) trade-offs on ASICs than this method, it is also more general in that it can target FPGAs *and* ASICs due to being integrated directly into Yosys. Nevertheless, it would appear that for the specific case of targeting the best PPA trade-offs for TMR on ASICs, the approach described in [16] is the most optimal one available.

2.4. Design-level approaches

Several authors have investigated applying TMR directly to HDL source code. One of the most notable examples was introduced by Kulis [18], through a tool he calls “TMRG”. TMRG operates on Verilog RTL by implementing the majority of a Verilog parser and elaborator from scratch. It takes as input Verilog RTL, as well as a selection of Verilog source comments that act as annotations to guide the tool on its behaviour. In turn, the tool modifies the design code and outputs processed Verilog RTL that implements TMR, as well as Synopsys Design Compiler design constraints. Like the goal of TaMaRa, the TMRG approach is designed to target both FPGAs and ASICs, and for FPGAs, Kulis correctly identifies the issue that not all FPGA blocks can be replicated. For example, a design that instantiates a PLL clock divider on an FPGA that only contains one PLL could not be replicated. Kulis also correctly identifies that optimisation-driven synthesis tools such as Yosys and Synopsys DC will eliminate TMR logic as part of the synthesis pipeline, as the redundancy is, by nature, redundant and subject to removal. In Yosys, this occurs specifically in the `opt_share` and `opt_clean` passes according to specific advice from the development team [4]. However, unlike Synopsys DC, Yosys is not constraint driven, which means that Kulis’ constraint-based approach to preserving TMR logic through optimisation would not work in this case. Finally, since TMRG re-implements the majority of a synthesis tool’s frontend (including the parser and elaborator), it is limited to only supporting Verilog. Yosys natively supports Verilog and some SystemVerilog, with plugins [19] providing more complete SV and VHDL support. Since TaMaRa uses Yosys’ existing frontend, it should be more reliable and useable with many more HDLs.

Lee et al. [20] present “TLegUp”, an extension to the prior “LegUp” High Level Synthesis (HLS) tool. As stated earlier in this document, modern FPGAs and ASICs are

typically designed using Hardware Description Languages (HDLs). HLS is an alternative approach that aims to synthesise FPGA/ASIC designs from high-level software source code, typically the C or C++ programming languages. On the background of TMR in FPGAs in general, the authors identify the necessity of “configuration scrubbing”, that is, the FPGA reconfiguring itself when one of the TMR voters detects a fault. Neither their TLegUp nor our TaMaRa will address this directly, instead, it’s usually best left up to the FPGA vendors themselves (additionally, TaMaRa targets ASICs which cannot be runtime reconfigured). Using voter insertion algorithms inspired by Johnson [9], the authors operate on LLVM Intermediate Representation (IR) code generated by the Clang compiler. By inserting voters before both the HLS and RTL synthesis processes have been run, cleverly the LegUp HLS system will account for the critical path delays introduced by the TMR process. This means that, in addition to performance benefits, pipelined TMR voters can be inserted. The authors also identify four major locations to insert voters: feedback paths from the datapath, FSMs, memory output signals and output ports on the top module. Although TaMaRa isn’t HLS-based, Yosys does have the ability to detect abstract features like FSMs, so we could potentially follow this methodology as well. The authors also perform functional simulation using Xilinx ISE, and a real-world simulation by using a Microblaze soft core to inject faults into various designs. They state TLegUp reduces the error rate by 9x, which could be further improved by using better placement algorithms. Despite the productivity gains, and in this case the benefits of pipelined voters, HLS does not come without its own issues. Lahti et al. [21] note that the quality of HLS results continues to be worse than those designed with RTL, and HLS generally does not see widespread industry usage in production designs. One other key limitation that Lee et al. do not fully address is the synthesis optimisation process incorrectly removing the redundant TMR logic. Their workaround is to disable “resource sharing options in Xilinx ISE to prevent sub-expression elimination”, but ideally we would not have to disable such a critical optimisation step just to implement TMR. TaMaRa aims to address this limitation by working with Yosys directly.

2.5. TMR verification

While Benites [13], [14] discusses verification of the automated TMR process, and other authors [6], [16], [20] also use various different verification/testing methodologies, there is also some literature that exclusively focuses on the verification aspect. Verification is one of the most important parts of this process due to the safety-critical nature of the devices TMR is typically deployed to. Additionally, there are interesting trade-offs between different verification methodologies, particularly fault injection vs. formal verification.

Beltrame [22] uses a divide and conquer approach for TMR netlist verification. Specifically, identifying limitations with prior fault-injection simulation and formal verification techniques, he presents an approach described as fault injection combined with formal verification: instead of simulating the entire netlist with timing accurate simulation, he uses a behavioural timeless simulation of small submodules (“logic cones”) extracted by automatic analysis. The algorithm then has three main phases:

1. Triplet identification: Determine all the FF (flip-flop) triplets present in each logic cone.
2. TMR structure analysis: Perform exhaustive fault injection on valid configurations.
3. Clock and reset tree verification: Assure that no FF triplets have common clock or set/reset lines.

This seems to be an effective and rigorous approach, as Beltrame mentions he was able to find TMR bugs in the radiation-hardened netlist of a LEON3 processor. Importantly, the code for the tool appears is available on GitHub as *InFault*. It would be highly worthwhile investigating the use of this tool for verification, as it has already been proven in prior research and may overall save time. That being said, a quick analysis of the code appears to reveal it to be “research quality” (i.e. zero documentation and seems partially unfinished). Another problematic issue is that the code does not seem to readily compile under a modern version of GCC or Clang, and would require manual fixing in order to do so. Finally, the *InFault* tool implements a custom Verilog frontend for reading designs. This has the exact same problem as Kulis’ [18] custom Verilog frontend: it’s not clear to what standard this is implemented. We may have to write a custom RTLIL or EDIF frontend to ingest Yosys netlists. The main question is whether resolving these issues would take more time than implementing formal verification ourselves in Yosys. One other important limitation not yet mentioned in Beltrame’s approach is the presence of false positives. Beltrame’s “splitting algorithm” requires a tunable threshold which, if set too low, may cause false positive detections of invalid TMR FFs. These false positives require manual inspection of the netlist graph in order to understand. This is extremely problematic for large designs, as it would seem to require many laborious hours from an engineer familiar with the *InFault* algorithm to determine if any given detection was a false positive or not. It’s also not immediately clear what the range of suitable thresholds for this value are that would prevent or possibly eliminate false positives.

Even if we do not end up using Beltrame’s [22] approach in its entirety (for example, if the false positives are a significant issue or if it’s too much work to read Yosys designs), we may nonetheless be able to repurpose parts of his work for TaMaRa. One aspect that would work particularly well inside of Yosys itself is step 3 from the algorithm, clock and reset tree verification. Yosys already has tools to identify clock and reset lines, so it should not be too much extra work to build a pass that verifies the clock and resets in the netlist are suitable for TMR. In addition, parts of Beltrame’s algorithm may be implementable using other Yosys formal verification tools, particularly SymbiYosys. His terminology as well, particularly the use of “logic cones”, will likely be critical in the development of TaMaRa.

2.6. Formal verification

Formal verification is increasingly being pursued in the development of FPGAs and ASICs as part of a comprehensive design verification methodology. The foundations for the formal verification of digital circuits extend back to traditional Boolean algebra and set theory in discrete mathematics. Building on these foundations, digital circuit

verification can be represented as a Boolean satisfiability (“SAT”) problem. The SAT problem asks us to prove whether or not there is a consistent assignment of input variables to a circuit to make the circuit evaluate to *true*. This forms the basic primitive, the underlying problem to solve, for nearly all circuit formal verification tasks; including both formal property verification and equivalence checking. Despite SAT’s usefulness, Karp [23] proved via the Cook-Levin theorem that it is an NP-complete problem (i.e. there is likely no polynomial time solution). Despite this, there exist a number of fast-enough SAT solvers [24], [25], that make the verification of Boolean circuits using SAT a tractable problem.

However, on large and complex designs, using SAT solvers directly on multi-bit buses can be slow. Instead, Satisfiability Modulo Theories (SMT) solvers can be used instead. SMT is a generalisation of SAT that introduces richer types such as bit vectors, integers, and reals [26]. Solving satisfiability modulo theories is still at least NP-complete, sometimes undecidable. Most SMT solvers either depend on or “call out” to an underlying SAT solver. One such SMT solver that uses this approach is Bitwuzla [27]. Others, however, such as Z3 [28] include their own SAT logic and other methods for computing solutions. The speed of SMT solvers is very important when performing formal verification of digital circuits, and there is a yearly SMT solving competition to encourage the development and analysis of high-performance SMT solvers [29].

Formal equivalence checking uses formal techniques to verify that two circuits are equivalent in functionality. Typically, circuits are partitioned into the *gate* circuit, which is the circuit to be verified, and the *gold* circuit, which is the reference model to be proved against. Equivalence is proved by constructing a Miter circuit, which is a type of circuit that uses the exclusive-OR (XOR) on the output of the gate and gold circuits. If the outputs of these XOR cells can be proved to be true, then the circuits are not equivalent [30]. In Yosys, this is achieved by using the `miter` command to automatically construct the equivalence circuit and insert formal assertions, which are then proved or disproved using an internal SAT solver via the `sat` command.

2.7. RTL fuzzing

In the software world, “fuzzing” refers to a process of randomly generating inputs designed to induce problematic behaviour in programs. Typically, fuzzing is started by referencing an initial corpus, and the program under test is then instrumented to add control flow tracking code. The goal of the fuzzer is to generate inputs such that the program reaches 100% instrumented branch coverage once the fuzzing process is completed.

While fuzzing is typically started from an initial corpus, there has also been interest in fuzzing languages directly without any initial examples, using information from the language’s grammar. One example is Holler’s LangFuzz [31], which uses a tree formed by the JavaScript grammar to generate random, but valid, JavaScript code. Mozilla developers have used LangFuzz successfully to find numerous bugs in their SpiderMonkey JavaScript engine. Generating code from the grammar directly also has the advantage

of making the fuzzing process significantly more efficient, as the fuzzer tool has the *a priori* knowledge necessary to “understand” the language. Compared to using a general purpose random fuzzer that typically generates and mutates test cases on a byte-by-byte basis [32], grammar fuzzers should be able to get significantly higher coverage of a target program much more efficiently.

Although these techniques are typically used for software projects, they can also be useful for hardware, particularly for EDA tools; given that Verilog is more or less just another programming language. RTL fuzzing is an emerging technique that can be useful to generate large-scale coverage of Verilog design files for EDA tools. Herklotz [33] describes “Verismith”, a tool capable of generating random and correct Verilog RTL. This is useful for TaMaRa verification, because it allows us to investigate *en masse* whether the tool changes the behaviour of the underlying circuit. It also allows us to quickly find, reproduce, minimise and fix challenging designs, which should hopefully lead to a more reliable algorithm with better coverage of industry-standard designs.

Chapter 3

Methodology

3.1. Concept

In the previous [Chapter 2](#), I presented a comprehensive literature review of existing automated TMR approaches. One of the main limitations that these algorithms have is that none are specifically integrated into the Yosys synthesis tool. I envision TaMaRa as a platform that provides a baseline TMR implementation that other researchers can extend upon, and that industry users can experiment with, all the while supporting both FPGAs/ASICs and being fully integrated as part of a widely used open-source EDA synthesis tool. Operating directly on Yosys' RTLIL intermediate representation ensures that any future optimisations Yosys gains, or any languages it supports in future, can be immediately also supported by TaMaRa.

To design the TaMaRa algorithm, I synthesise existing approaches from the literature review to form a novel approach suitable for implementation in Yosys. Specifically, I synthesise the voter insertion algorithms of Johnson [\[9\]](#), the RTL annotation-driven approach of Kulis [\[18\]](#), and parts of the verification methodology of Benites [\[13\]](#) and Beltrame [\[22\]](#), to form the TaMaRa algorithm and verification methodology. Based on the dichotomy identified in [Chapter 2.1](#), TaMaRa will be classified as a *netlist-level* approach, as the algorithms are designed by treating the design as a circuit (rather than HDL).

I propose a modification to the synthesis flow that inserts TaMaRa before technology mapping. This means that the circuit can be processed at a low level, with less concerns about optimisation removing the redundant TMR logic, as has been observed in other approaches [\[20\]](#) and through conversation with the Yosys developers [\[4\]](#). However, some Yosys synthesis scripts do perform additional optimisation *after* technology mapping, which again risks the removal of the TMR logic. Yet, we also cannot operate after technology mapping, since TaMaRa voter circuits are described using relatively high level circuit primitives (AND gates, NOT gates, etc) instead of vendor-specific FPGA primitives like LUTs. The best solution to this likely involves an upstream modification to Yosys that allows for certain optimisation passes to be selectively skipped; this is further discussed in [Chapter 5.1](#).

Whilst TaMaRa aims to be compatible with all existing designs with minimal changes, some preconditions are necessary for the algorithm to process the circuit correctly.

Since the algorithm is intended to work with all possible circuits, it cannot predict what the end user wants to do with the voter error signal (if anything). As discussed in the

literature review, the typical use case for the error signal is to perform configuration scrubbing when upsets are detected. This, however, is a highly vendor-specific process for FPGAs, and is not at all possible on ASICs. To solve this problem, TaMaRa does not aim to provide configuration scrubbing directly, instead leaving this for the end user. Instead, the end user can attach an HDL annotation to indicate an output port on a module that TaMaRa should wire a global voter error signal to. In SystemVerilog, this uses the `(* tamara_error_sink *)` annotation, as shown in [Listing 1](#):

```
module my_module(  
    input logic a,  
    (* tamara_error_sink *)  
    output logic err  
);
```

Listing 1: Usage of the `(* tamara_error_sink *)` annotation

End users are then free to implement configuration scrubbing using the tool and methodology appropriate to their platform.

Additionally, while TaMaRa aims to require minimal or no changes to the circuit itself, there are changes necessary to the synthesis pipeline. Unlike in normal Yosys synthesis scripts, the design cannot be lowered directly to FPGA/ASIC primitives (LUTs, standard cells, etc). It first needs to be lowered to abstract logic primitives (AND gates, NOT gates, etc) that TaMaRa can process, particularly, that it can generate voter circuits in. Then, TaMaRa can be run, after which the design can be lowered to FPGA primitives or ASIC standard cells. TaMaRa currently also requires the user to run the `splitcells` and `splitnets` commands before it is invoked to split apart multi-bit buses and cells, which are not yet directly supported. These additional requirements may introduce a slight area overhead, but it would be possible to eliminate them in the future through better algorithm design.

3.2. Implementation

Over the course of this thesis, TaMaRa was successfully written from the ground up as a Yosys plugin. This plugin consists of around 2,300 lines of C++20, and introduces one new command to Yosys: `tamara_tmr`.

TaMaRa is currently designed to only operate on one module, that being the top module. This is typical of space applications. For example, consider a Verilog top module called `cpu_top` that contains a 32-bit RISC-V CPU, along with its register file, ALU, memory and instruction decoder. To ensure full rad-hard reliability in space, the whole `cpu_top` module needs to be triplicated. However, in the future, it would be a nice feature to be able to have finer grained control over the parts of the design are triplicated. This does unfortunately introduce some significant problems that will be elaborated on later.

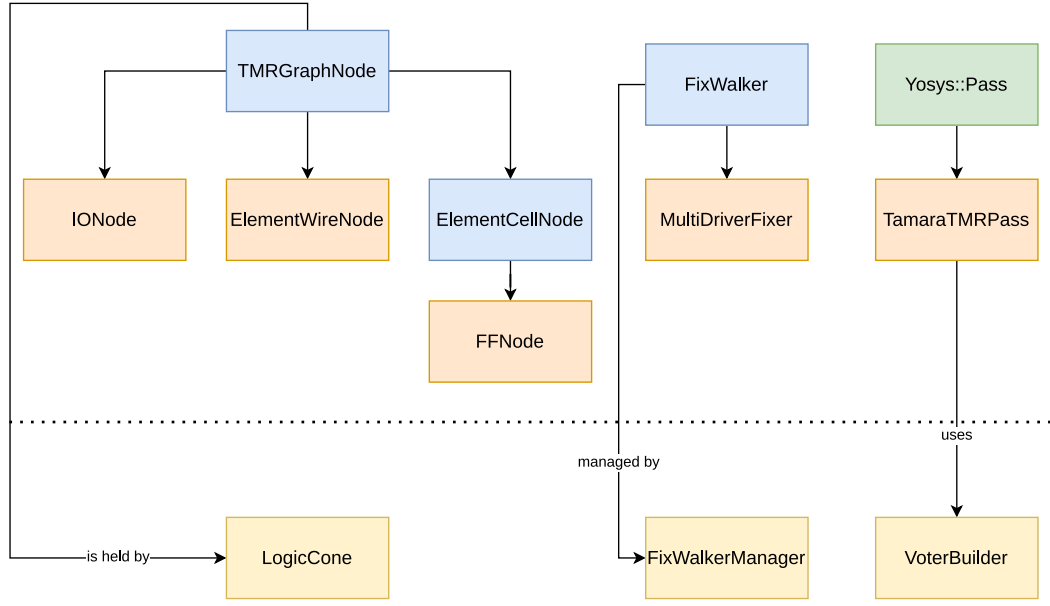


Figure 3: Class diagram of the TaMaRa codebase

TaMaRa consists of multiple C++ classes (Figure 3). Broadly speaking, these classes combine together to form the following algorithm. This is also shown in Figure 11.

3.2.1. Voter design

Voters are one of the most important parts of a TMR circuit, and so I believed it was extremely important to design them and verify them with a high degree of assurance. In the very beginning, the voter circuit was designed manually; first by sketching the truth table by hand, then automatically converting this to a logic schematic using Logisim Evolution [34]. The Logisim circuit was then transformed manually into a series of C++ macros that build an equivalent circuit in RTLIL. A formal equivalence check was performed between this RTLIL design and the original truth table sketched by hand, which was correct.

Given the single-bit inputs a , b , c , and the single-bit outputs out and err , the truth table for a majority voter can be described as follows (Table 1):

a	b	c	out	err
0	0	0	0	0
0	0	1	0	1
0	1	0	0	1
0	1	1	1	1
1	0	0	0	1
1	0	1	1	1
1	1	0	1	1
1	1	1	1	0

Table 1: Truth table for a single-bit majority voter

Using techniques such as Karnaugh mapping [35], this truth table can be optimally mapped to a combinatorial circuit. In this case, Logisim Evolution [34] was used, which produced the following result as shown in Figure 4. This circuit consists of 3 NOT gates, 6 AND gates, and 4 OR gates. These are all two-input gates.

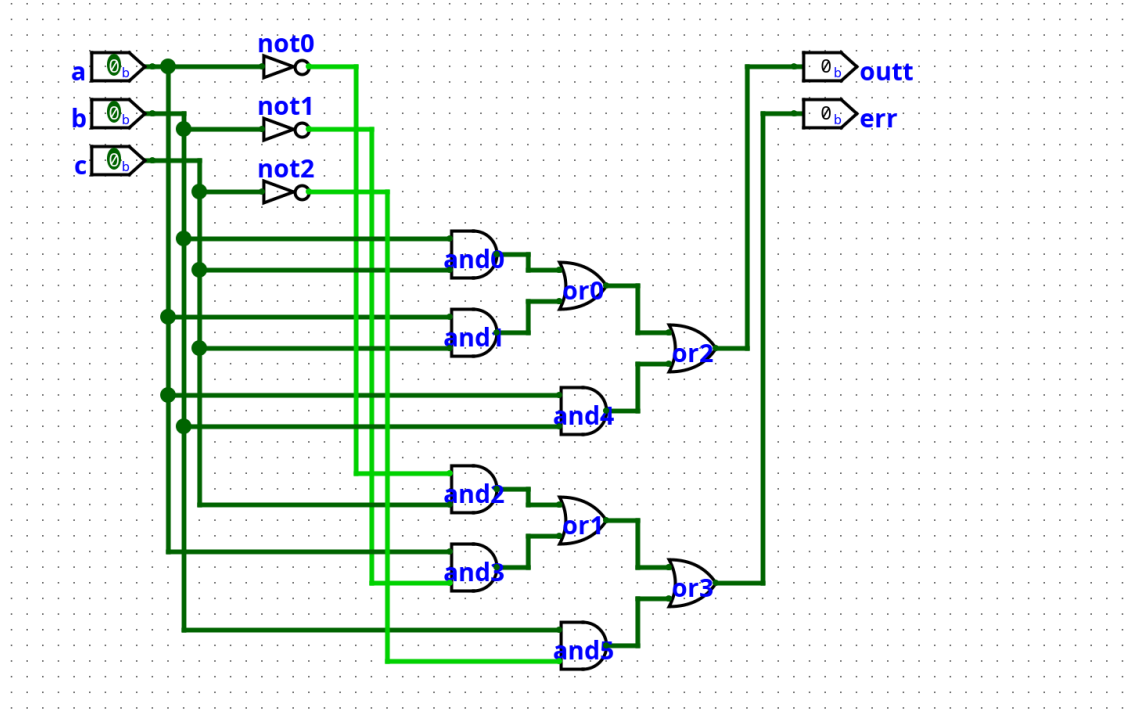


Figure 4: Logisim Evolution schematic for voter circuit

Using a series of macros, this can be translated into C++ code that generates RTLIL circuits. First, we define a series of macros like WIRE, NOT, AND and OR that add RTLIL objects to the current module with the correct tamara_voter annotation, which is expected to be applied to all voter logic elements. Then, I performed a direct, manual translation as shown in Listing 2:

```

// NOT
// a -> not0 -> and2
WIRE(not0, and2);
NOT(0, a, not0_and2_wire);

// b -> not1 -> and3
WIRE(not1, and3);
NOT(1, b, not1_and3_wire);

// c -> not2 -> and5
WIRE(not2, and5);
NOT(2, c, not2_and5_wire);

// AND
// b, c -> and0 -> or0
WIRE(and0, or0);
AND(0, b, c, and0_or0_wire);

// a, c -> and1 -> or0
WIRE(and1, or0);
AND(1, a, c, and1_or0_wire);

// and so on, and so on...

```

Listing 2: Partial listing of C++ macros to generate voter

When applied in Yosys, a schematic similar to the Logisim circuit is generated, as shown in Figure 5:

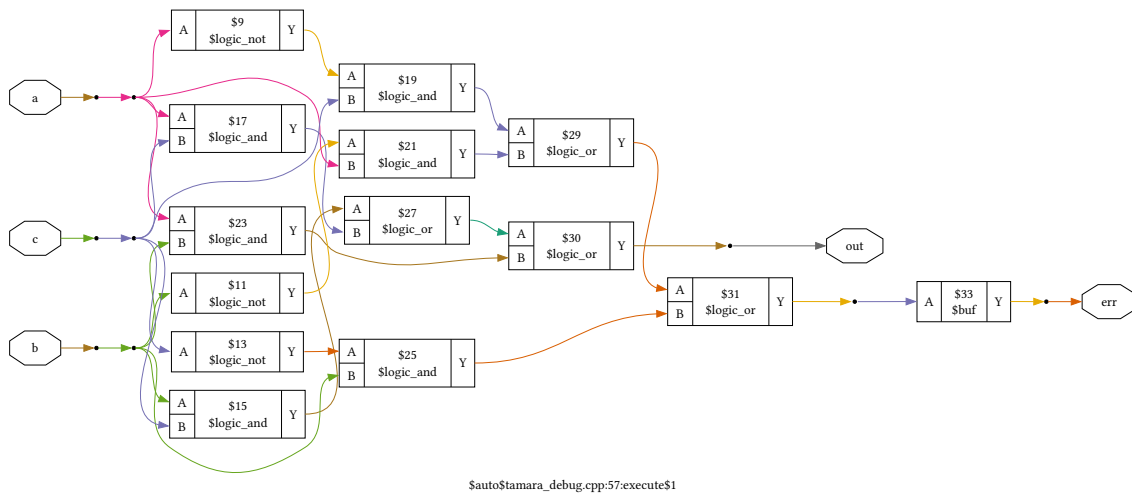


Figure 5: Voter schematic generated by Yosys

Using a SystemVerilog translation of the Boolean function implementing a voter (Listing 3), the RTLIL generated voter was formally verified to be correctly implemented. Further details on the formal verification procedure are presented later in Chapter 3.3.2.

```

module voter(
    input logic a,
    input logic b,
    input logic c,
    output logic out,
    output logic err
);
    assign out = (a && b) || (b && c) || (a && c);
    assign err = (!a && c) || (a && !b) || (b && !c);
endmodule

```

Listing 3: SystemVerilog implementation of 1-bit majority voter

3.2.2. RTLIL netlist analysis

In Yosys, although RTLIL is used to model the netlist, the connections between cells and wires are not immediately available for use in TaMaRa. Instead, we first perform a topological analysis of all the cells and wires in the netlist. We consider output and input ports for cells, and also uniquely consider wires as well. The aim is to construct a `tamara::RTLILWireConnections` object, which is a mapping between the name of a wire or cell (which is guaranteed to be unique in an RTLIL design), and the set of wires or cells it may be connected to on a backwards traversal. The last element is important, because this data structure also acts as an efficient cache to use when searching the circuit on a backwards-BFS. During this step, we also construct other similar data structures that are used to lookup `RTLIL::SigSpec` objects, which are unique in RTLIL and can be used to represent RTL concepts like constants and wires. An example of this construction is shown in [Figure 6](#).

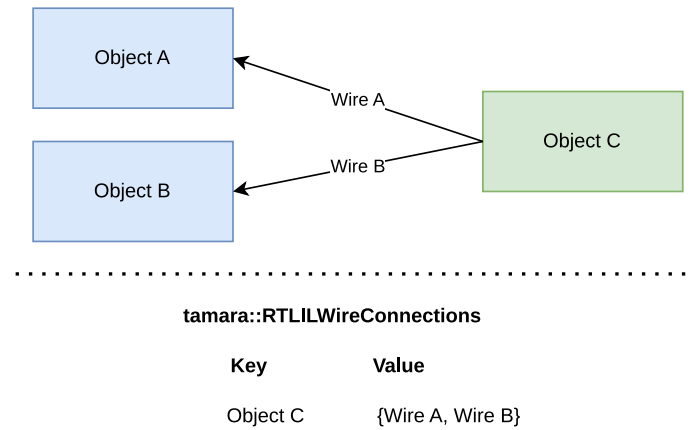


Figure 6: Demonstration of RTLILWireConnections construction

3.2.3. Backwards breadth-first search

The key step of the TaMaRa algorithm is mapping out and tracking the combinatorial logic primitives that are located in between sequential logic primitives in a given design. This enables us to correctly replicate the design, without introducing sequential delays that would invalidate the circuit's design. In order to achieve this, I perform a breadth-first search (BFS) search, operating backwards *from* the output of the circuit *towards*

the input of the circuit. The reason we operate backwards is under the assumption that the *outputs* of a circuit naturally depend on both the combinatorial and sequential path through the circuit; so, by working from outputs backwards to inputs, we naturally cover only the essential circuit elements and guarantee we won't miss anything. This is the same approach used by Beltrame [22].

On the backwards BFS, when we reach a flip-flop or an IO node (i.e. an input to the circuit), we wrap up the search² and declare the current collected RTLIL primitives as part of a single *logic cone*.

TaMaRa's definition of a logic cone is shown in Figure 7. The first combinatorial logic cone is shown in blue, the second in green; both of these would be discovered separately by the backwards BFS.

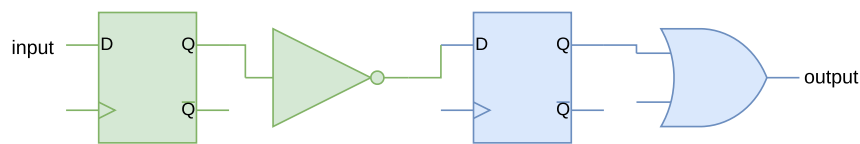


Figure 7: Description of TaMaRa's definition of logic cones

3.2.4. Combinatorial replication

Once we have formed a logic cone, we are able to replicate all of the components inside it. This is a relatively trivial operation and is simply a matter of using the Yosys API to instantiate two replicas for each original node. These replicas are also marked with special TaMaRa annotations to indicate that they are replicas, and what logic cone they belong to.

3.2.5. Voter insertion

With the combinatorial primitives in the circuit replicated, the next step is to generate and insert majority voters to vote on the redundant logic, and thereby actually implement TMR.

TaMaRa voters are always single-bit. Handling multi-bit signals is a two-stage process. Firstly, before TaMaRa is run, the user is required to run the `splitcells` and `splitnets` commands, which break multi-bit cells and multi-bit wires respectively into multiple single-bit instances. Whilst this handles most of the internals of the circuit, the inputs/outputs to the circuit will still be multi-bit. For example, consider a module with an input `logic [3:0] a;` the port `a` will still be 4-bits wide. To work with this, the voter generator is able to split apart these multi-bit signals and attach a unique voter for each bit. When these chains are built, the voter builder dynamically inserts a Yosys `$reduce_or` cell to OR together all signals from all voters. The voter builder is able to detect when this cell is necessary or not, and if it's not necessary, emits a `$buf` cell to improve PPA.

TODO talk about the err signal in more detail

²This is not quite the same as terminating the search immediately; it's important that we consider remaining items in the BFS queue before instantly terminating the search.

For multi-cone designs, the voter builder is also capable of building a tree structure of OR gates to bubble up the individual voter error signals to a global error signal. It is worth noting that this tree-like structure will significantly increase the combinatorial critical path delay of the circuit, and it would be better replaced with more optimal structures in future work.

On any given logic cone, we define the “voter cut point” to be the location in the logic cone netlist where we should splice the circuit and insert the majority voter. Currently, TaMaRa determines the voter cut point during the backwards BFS. It is set to be the first node encountered on the backwards BFS that fulfills the following criteria:

- It is not the very first node in the entire backwards BFS (i.e. this would be the output cell); and
- It is not a *terminal node* (i.e. not an `IONode` or an `FFNode`); and
- It is not an `ElementWireNode`

The voter cut point is set once and only once per node. Once it is set, it’s not immediately used by the backwards BFS, but rather passed onto the wiring stage for later use.

TODO Yosys 'show' result of VoterBuilder OR chain and \$reduce_or

3.2.6. Wiring

The most complex (and error prone) element of the TaMaRa algorithm is, by far, the wiring logic. As a generalised representation of RTL at various stages of synthesis, RTLIL is extremely complex. Handling complex, recurrent, multi-bit circuits with elements like bit-selects, slicing and splicing is very challenging. TaMaRa approaches this on a “best effort” basis, but is currently unable to handle all wiring types present in Yosys. In essence, the wiring logic is similar to performing “surgery” on the circuit; cutting and splicing complicated RTLIL primitives that can be challenging to re-attach correctly. The wiring logic remains the single biggest limitation in the TaMaRa algorithm, and is often the sole reason that more complex circuits cannot yet be processed.

The first step of the wiring process is to insert the majority voter, which was covered separately in the prior section [Chapter 3.2.5](#). Specifically, the voter cut point is determined from the earlier backwards BFS stage, and a procedure³ is used to extract the correct wires from replicated elements in the circuit to use as the A, B, C, OUT and ERR ports of the voter. This is then passed to the voter inserter to insert directly into the circuit.

Once the voter has been inserted, and holding a reference to the RTLIL output wire of the circuit, the set of RTLIL `SigSpecs` attached to the output wire are located. This is mainly used to determine if multiple wires, bits, chunks or other similarly complex RTLIL primitives are attached to the wire. If there is only one single `SigSpec` attached, then wiring logic “stitches together” the voter output port directly to the original circuit. If there are multiple `SigSpecs`, then the wiring logic finds the `SigSpecs` that are attached to the *output* of the voter on the *original* circuit before modification. Then, it stitches

³It should be noted that this procedure is one of the largest causes of errors and other crashes in circuit processing, and should likely be overhauled in future work.

together this original `SigSpec` and the rest of the circuit. This is a very large (and poor) assumption, so we also warn the user if our assumptions do not hold; for example, if there are *multiple* `SigSpecs` originally attached to the voter output wire, which is currently not handled.

TODO decision tree or similar

3.2.7. Wiring fix-up

TaMaRa’s wiring logic currently cannot handle the entire circuit in a single pass. Hence, TaMaRa wiring cannot simply be done in a single stage. Instead, a multi-stage process was developed that uses a second pass to detect and “fix-up” cases of invalid wiring. This is achieved by sub-classing a `tamara::FixWalker` interface, which is in turn processed by a `tamara::FixWalkerManager`. This utility walks the RTLIL circuit using the visitor pattern [36], and invokes methods on the `tamara::FixWalker` accordingly.

At present, the main problem to fix up is situations in which cells can have multiple drivers. This occurs when replicating wires connecting the cells. A second pass is necessary in order to correctly connect the replicated wires to the replicated cells. This special case is detected by a `tamara::FixWalker` instance that specifically looks for cells:

- Which are driven by 3 wires; and
- Which drive 3 wires; and
- Where each of the driven wires have a (`* tamara_cone *`) annotation (i.e. they have been replicated by TaMaRa); and
- Where each of the driver wires have a (`* tamara_cone *`) annotation

Figure 8 shows the schematic of a circuit before the multi-driver fixer described above was run. From the schematic, it is clear that the `ff` wire has multiple drivers, and drives multiple cells.

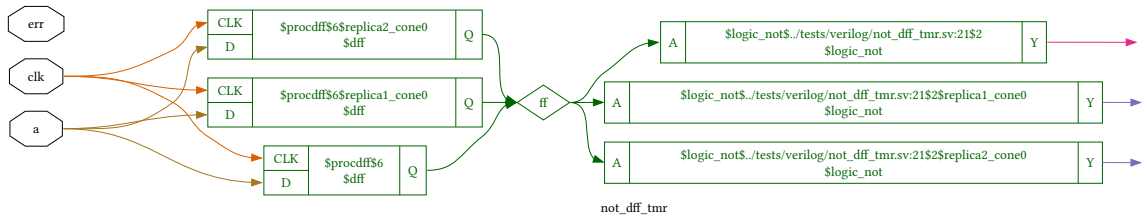


Figure 8: Schematic of circuit before running the multi-driver fixer

After running the multi-driver fixer, Figure 9 shows that the multi-driver cell has been detected and repaired successfully.

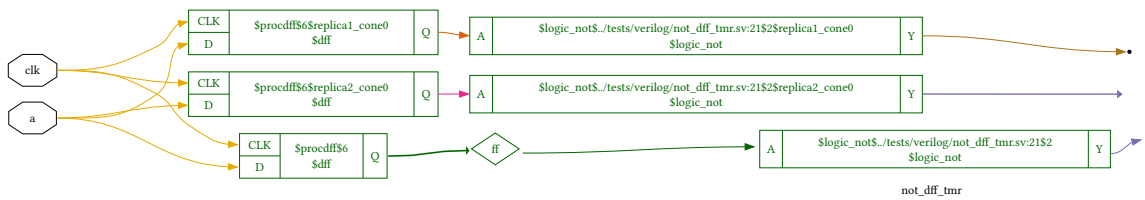


Figure 9: Schematic of circuit after running the multi-driver fixer

3.2.8. Search continuation

For multi-cone circuits with more than one logic cone between the inputs and outputs, the algorithm needs to continue analysing the circuit. During the search stage as described in [Chapter 3.2.3](#), there is an additional step where the TaMaRa algorithm checks for successor logic cones and therefore if a continued search is required.

During the search, if the input node of a logic cone is connected to other cells, and those cells have not yet been explored as part of a previous search, then the input node is added to a queue of successor nodes. These successor nodes are searched using exact same process, essentially taking the algorithm back to [Chapter 3.2.3](#), and repeating until no more successor nodes remain (i.e. the input of the circuit is reached). This is further illustrated in [Figure 10](#).

A global set of successor nodes that have been already explored is maintained, so that recurrent circuits do not produce infinite searching loops.

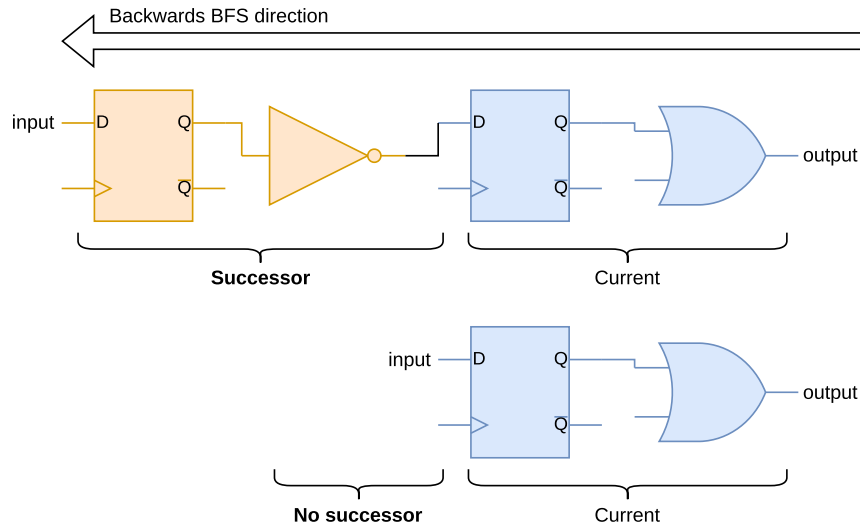


Figure 10: Demonstration of search continuation for two circuits

3.2.9. Summary

In summary, the algorithm can be briefly described as follows:

1. Analyse the RTLIL netlist to generate `tamara::RTLILWireConnections` mapping; which is a mapping between an RTLIL Cell or Wire and the other Cells or Wires it may be connected to.
2. For each output port in the top module:
 1. Perform a backwards breadth-first search through the RTLIL netlist to form a logic cone
 2. Replicate all combinatorial RTLIL primitives inside the logic cone
 3. Generate and insert the necessary voter(s) for each bit
 4. Wire up the newly formed netlist, including connected the voters

3. Perform any necessary fixes to the wiring, if required
4. With the initial search complete, compute any follow on/successor logic cones from the initial terminals
5. Repeat step 2 but for each successor logic cone
6. Continue until no more successors remain

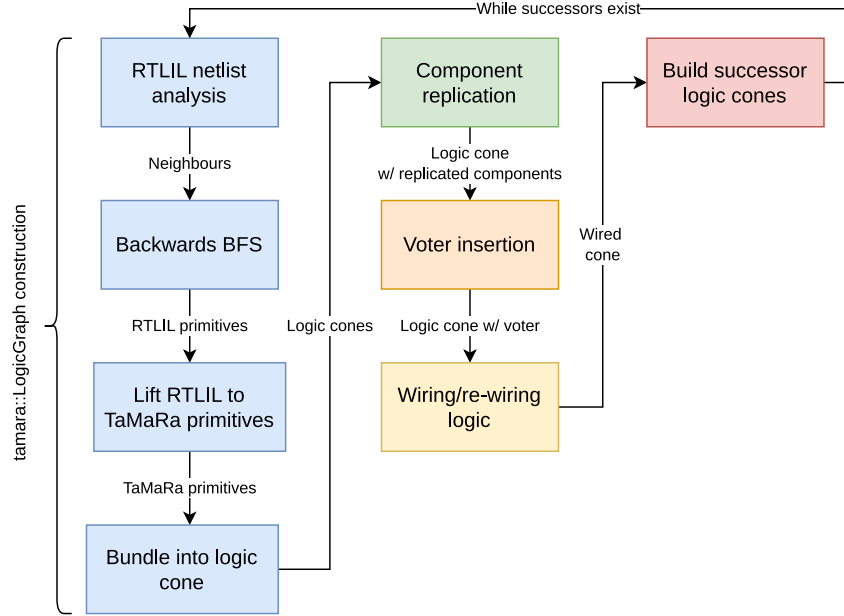


Figure 11: Logic flow of the TaMaRa TMR algorithm

In general, the TaMaRa code is designed to be robust to any and all user inputs, and easy to debug when the algorithm does not work as expected. This is achieved by a combination of detailed, friendly error reporting and copious assert statements available in debug builds. For example, if a user specifies an error port marked (`* tamara_error_sink *`) that is multi-bit, which is not supported, TaMaRa will print an error explaining this in detail. The algorithm also performs self-checking using assert statements throughout the process to catch internal errors that may occur.

The friendly error reporting is designed as a “first line of defence” for the most common user errors, and the addition of asserts plays an important role in debugging end user crashes. Ideally, TaMaRa will rather crash than generate an impossible design. All of this combines together to hopefully make a tool that users can be confident deploying in rad-hardened, safety critical scenarios.

3.3. Verification

Due to its potential for use in safety critical sectors like aerospace and defence, comprehensive verification and testing of the TaMaRa flow is extremely important in this thesis. We want to verify to a very high level of accuracy that TaMaRa both works by preventing SEUs to an acceptable standard, and also does not change the underlying behaviour of the circuits it processes.

TaMaRa is a highly complex project that, during the course of this one year thesis, developed into a substantial and complicated codebase. Not only is the TaMaRa algorithm itself complex, but it is also dependent on top of the very complex Yosys codebase. In addition, the very process of EDA synthesis is highly non-trivial; in some ways, akin to writing a compiler. This means that an extensive verification methodology is required not just as a once-off, but throughout development.

To ensure this verification could be achieved, I implemented a regression test suite, which is common in large-scale software projects. The regression test script is written in Python, and reads the list of tests to run from a YAML document. This script is capable of running both Yosys script tests as well as formal equivalence checking tests using the `eqy` tool. The script also keeps track of prior results and recently failed tests, so that regressions can be easily detected. This tool was an essential part of the TaMaRa development process, as it allowed major refactors to be performed without the worry of breaking any prior tests.

3.3.1. Manual verification

The design and use of RTL testbenches has, and continues to be important when designing FPGA and ASIC projects. Likewise, RTL testbenches are very important when designing EDA tools. Compared to FPGA/ASIC design, when working on EDA tools, having a representative sample of a large number of projects is the most important aspect. For TaMaRa, I sourced a number of representative small open-source Verilog projects with acceptable licences for inclusion in the `test` directory. These designs include:

- Various cyclic redundancy check (CRC) calculators of varying bit-depths
 - Tests TaMaRa’s handling of combinatorial circuits
- Small RISC-V CPUs: `picorv32`, `femtorv32`, `minimax`, Browndeer Technologies’ `rv8`
 - CPUs are highly representative of large Verilog projects, and include complex combinatorial and sequential circuits

In addition, I also wrote a number of much smaller testbenches to target specific bugs or specific features in TaMaRa. These were very important in the initial development and verification of the algorithm, as their tiny size allowed for visual debugging using Yosys’ `show` command. These circuits are documented in full in [Chapter 4.1](#).

3.3.2. Formal verification

For TaMaRa specifically, formal verification is abstracted through the use of Yosys’ `eqy` tool, and by extension its usage of the `sby`(SymbiYosys) tool. `eqy` is used for formal equivalence checking between two circuits, and is responsible for partitioning the input circuit to a form suitable for equivalence checking. This is then sent on to `sby`, which in turn transforms the circuit into a suitable SMT proof for an SMT solver. TaMaRa was going to use the Bitwuzla [\[27\]](#) solver, but due to upstream issues with both Yosys and Bitwuzla, settled for using the industry standard Yices [\[37\]](#), which is quite fast. Yosys also features a `mutate` command that was originally written to verify the correctness of

self-checking testbenches. Essentially, it injects faults into a design and verifies that the self-checking testbench correctly flags these mutated designs as invalid.

TODO talk about the miter and sat proof commands which we use instead

The purpose of applying equivalence checking to the TaMaRa verification flow is to formally prove (for specific circuits, at least) that the tool holds up two of its key guarantees: that it does not change the underlying behaviour of the circuit during processing, and that it actually protects the circuit from SEUs. We could also check this using testbenches, or for simple combinatorial circuits by comparing the truth table manually, but SMT-based formal equivalence checking supports all circuit types and is more robust and reliable. If the formal equivalence check passes, we can be absolutely certain that the behaviour of the circuit has not changed, for all possible inputs; and for sequential circuits, for all possible inputs *and* all possible states.

The first guarantee, that the TaMaRa algorithm does not change the behaviour of the circuit, can be verified directly by using the formal equivalence checker and SMT solver. However, verifying the second guarantee - that TaMaRa actually protects against SEUs - is more challenging. To this, I devised a method that combines the `mutate` command with the equivalence checker. The *gold* circuit (the circuit to be verified against) is set to be the original design, with no faults and no TaMaRa replicas. The *gate* circuit (the circuit that is being verified) is set to the original circuit, with TaMaRa replicas, and then with a certain number of mutations. This methodology operates under the realisation that if the replicated circuit correctly masks faults, it should then also have the same behaviour as the non-replicated circuit minus the faults.

3.3.3. RTL fuzzing techniques

As mentioned in [Chapter 2.7](#), RTL fuzzing is an emerging technique for generating large-scale coverage of Verilog design files for EDA tools. Hence, part of the TaMaRa verification flow involves using Verismith [\[33\]](#) to generate small random Verilog designs, and running TaMaRa end-to-end on these designs. Initially, we will be looking for crashes, assert failures and memory errors using AddressSanitizer, but later we will also use Yosys' `eqy` tool to prove that the designs stay the same before and after TaMaRa runs. Using the GNU Parallel tool, this work can be trivially distributed across multiple cores. Running TaMaRa with the Verismith fuzzer on 8192 small designs takes around 5 minutes on an AMD Ryzen 9 5950X workstation.

To simplify the above, a shell script was developed to run this process end-to-end, and automatically clean up tests that did not fail; leaving only failed tests left over. With automatic timestamped directories, this is potentially a tool that could run as part of a continuous integration (CI) workflow for automatic validation.

Chapter 4

Results

4.1. Testbench suite

In order to test the TaMaRa algorithm, a number of SystemVerilog testbenches implementing various different types of circuits were designed. This section will detail the testbench suite in full. In each of the selections below, the attached table shows the circuit name, the SystemVerilog RTL describing the circuit, and its schematic after running the following Yosys script:

```
read_verilog -sv $name
prep
splitcells
splitnets
show -colors 420 -format svg -prefix $output
```

This list approaches circuits in their order of complexity: first starting with simple, single-bit combinatorial circuits, and then progressing up to advanced, multi-bit, multi-cone, recurrent, sequential circuits. This was also the order in which the TaMaRa algorithm was verified: starting with small, simple circuits, and progressing to complex ones, verifying incrementally along the way.

4.1.1. Combinatorial circuits

The simplest type of digital circuit is a single-bit, purely combinatorial one. [Table 2](#) lists these single-bit combinatorial circuits. These were critical for initial, early implementation of the TaMaRa algorithm, as their small size allowed for visual debugging using the Yosys show tool.

Name	SystemVerilog RTL	Synthesised schematic
not	<pre>module inverter(input logic a, output logic o, (* tamara_error_sink *) output logic err); assign o = !a; endmodule</pre>	
not_slice	<pre>module not_slice(input logic a, input logic b, output logic[1:0] out, (* tamara_error_sink *) output logic err);</pre>	

	<pre> assign out = { !a, !b }; endmodule </pre>	
not_swizzle_low	<pre> module not_swizzle_low(input logic a, output logic[1:0] out, (* tamara_error_sink *) output logic err); assign out = { !a, 1'd0 }; endmodule </pre>	
not_swizzle_high	<pre> module not_swizzle_high(input logic a, output logic[1:0] out, (* tamara_error_sink *) output logic err); assign out = { 1'd0, !a }; endmodule </pre>	
mux_1bit	<pre> module mux_1bit(input logic a, input logic b, input logic sel, output logic o); assign o = sel ? a : b; endmodule </pre>	

Table 2: Table of single-bit combinational circuit designs

4.1.2. Multi-bit combinational circuits

Once the single-bit combinational circuits were confirmed to be working, the next set of tests involves multi-bit combinational circuits, as shown in Table 3. This is useful to ensure that the voter builder, as described in Chapter 3.2.5, correctly inserts a voter for each bit in the bus; and also that the wiring code can handle multi-bit edge signals.

Name	SystemVerilog RTL	Synthesised schematic
not_2bit	<pre> module inverter(input logic[1:0] a, output logic[1:0] o, (* tamara_error_sink *) output logic err); assign o = ~a; endmodule </pre>	
not_32bit	<pre> module inverter(input logic[31:0] a, output logic[31:0] o, (* tamara_error_sink *) output logic err); assign o = ~a; endmodule </pre>	<p><i>Identical to above</i></p>

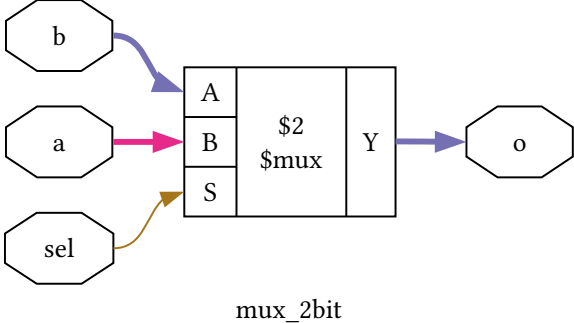
mux_2bit	<pre> module mux_2bit(input logic[1:0] a, input logic[1:0] b, input logic sel, output logic[1:0] o); assign o = sel ? a : b; endmodule </pre>	 <p style="text-align: center;">mux_2bit</p>
----------	---------------------------------------------------------------------------------------------------------------------------------------------------------------------	--------------------------------------------------------------------------------------------------------------------------------

Table 3: Table of multi-bit combinatorial circuit designs

4.1.3. Sequential circuits

In the previous sections, the testbenches were all combinatorial circuits, and did not use sequential elements such as D-flip-flops. Combinatorial circuits are easy to design and especially easy to verify, but are not at all representative of the majority of complex SystemVerilog designs. Both Yosys’ formal verification tools, and the underlying Yices [37] SMT solver support sequential circuits, and they form a valuable part of the testbench suite. Additionally, sequential circuits involve a clock signal, where the TaMaRa algorithm must be careful to connect the clock signal correctly to the TMR replicas. These testbenches are shown in Table 4.

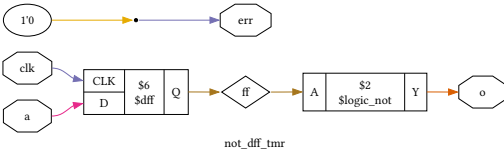
Name	SystemVerilog RTL	Synthesised schematic
not_dff_tmr	<pre> module not_dff_tmr(input logic a, input logic clk, output logic o, output logic err); logic ff = 0; always_ff @(posedge clk) begin ff <= a; end assign o = !ff; endmodule </pre>	 <p style="text-align: center;">not_dff_tmr</p>

Table 4: Table of sequential circuit designs

4.1.4. Multi-cone circuits

Whilst sequential circuits more accurately represent complex industry designs than combinatorial circuits, they are still not adequate test-cases for even the simplest industry designs. These designs typically connect together multiple sequential circuits in a pipeline. These circuits challenge TaMaRa’s multi-cone capabilities, and additionally it’s multi-voter insertion methodology. In the most complex case, it is possible to have multi-cone, multi-voter, multi-bit circuits. These multi-cone designs are shown in Table 5.

Name	SystemVerilog RTL	Synthesised schematic
cones	<pre> module cones(input logic a, input logic clk, output logic out); logic stage1; logic stage2; always_ff @(posedge clk) begin stage1 <= !a; end always_ff @(posedge clk) begin stage2 <= !stage1; end assign out = stage2; endmodule </pre>	
cones_min	<pre> module cones_min(input logic a, input logic clk, output logic out); logic stage1; always_ff @(posedge clk) begin stage1 <= !a; end assign out = !stage1; endmodule </pre>	
cones_2bit	<pre> module cones_2bit(input logic[1:0] a, input logic clk, output logic[1:0] out); logic[1:0] stage1; logic[1:0] stage2; always_ff @(posedge clk) begin stage1 <= ~a; end always_ff @(posedge clk) begin stage2 <= ~stage1; end assign out = stage2; endmodule </pre>	

Table 5: Table of multi-cone circuits

4.1.5. Feedback circuits

TODO

Name	SystemVerilog RTL	Synthesised schematic
recurrent_dff	<pre> module recurrent_dff (input logic clk, output logic q); always_ff @(posedge clk) begin q <= ~q; end endmodule </pre>	

Table 6: Table of feedback circuits

4.2. Formal verification

4.2.1. Equivalence checking

- Unsure how to systematically show equivalence checking results?
- Maybe by the numbers?

4.2.2. Fault injection

- Description of fault injection setup, some circuit diagrams, and proof that it passes the formal verification
- Establish a baseline to prove that fault injection on an unprotected circuit has 0 percent mitigated faults

4.2.3. Fault injection studies: Protected voter

I propose two main classes of fault injection studies. In the first class of tests, known as “Protected voter tests”, the voter circuit itself is ignored and not subject to faults. Whilst this is unrepresentative of real-world faults, it enables us to explore the validity of the voter circuit on its own. Particularly, it enables us to formally verify that the voter is able to protect a given circuit against a wide variety of faults, and to understand how many faults this is before the test fails.

Ignoring the voter circuit was accomplished through the Yosys script in [Listing 4](#). The TaMaRa algorithm annotates each cell and wire that is part of the voter with the `tamara_voter` RTLIL annotation.

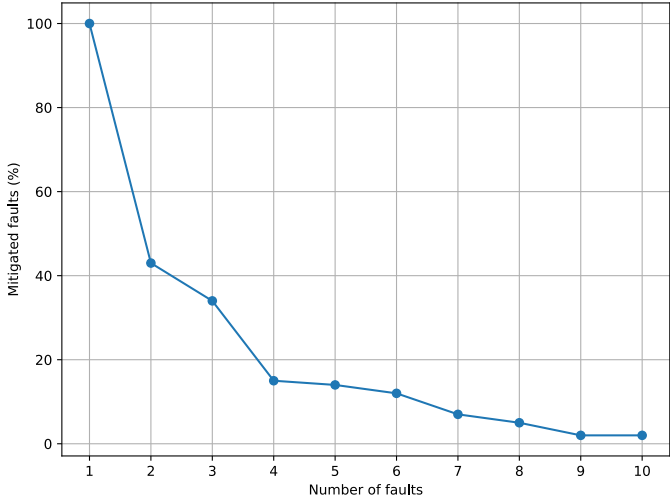
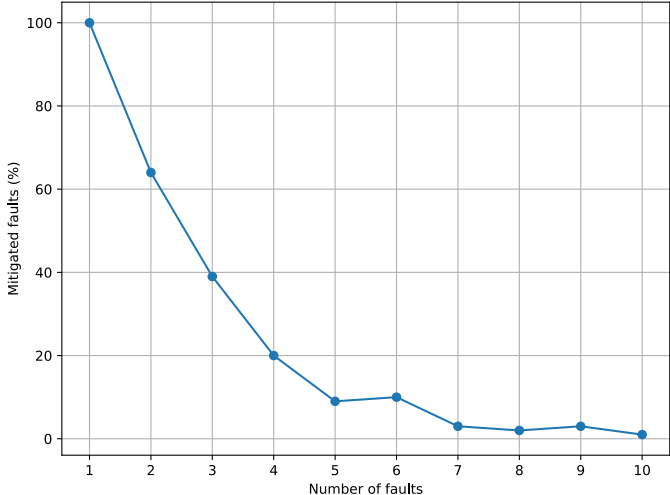
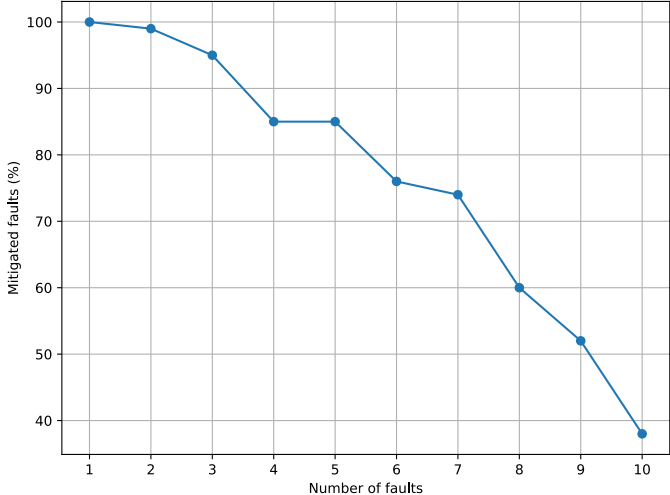
```

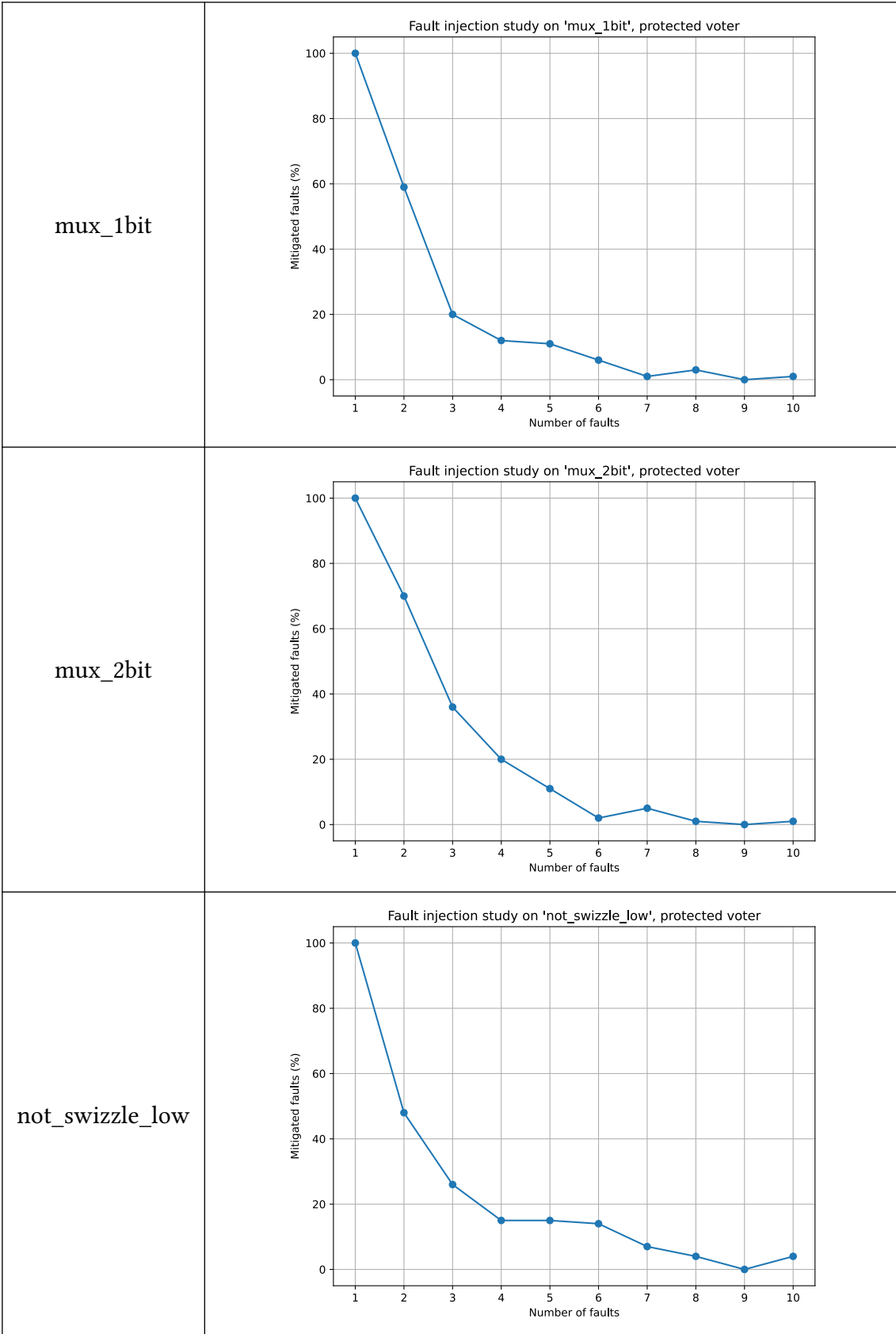
# select only input signals
select % a:tamara_voter %d
# apply a random mutation (fault injection)
mutate -list {faults} -seed {seed} -o /tmp/tamara_fault_injection
# deselect, go back to top module
select -clear
# execute the fault injection command
script /tmp/tamara_fault_injection

```

Listing 4: Yosys script to deselect TaMaRa voter wires/cells

[Table 7](#) presents the results for this protected voter fault-injection study. As the fault injection process is stochastic, it uses a sample of 100 runs per fault. The circuits listed in this table correspond to the suite of circuits presented in [Table 2](#), after they have been processed end-to-end correctly by the TaMaRa algorithm.

Circuit name	Fault injection results																						
not_tmr	<p data-bbox="746 293 1158 315">Fault injection study on 'not_tmr', protected voter</p>  <table border="1" data-bbox="587 315 1259 808"> <thead> <tr> <th>Number of faults</th> <th>Mitigated faults (%)</th> </tr> </thead> <tbody> <tr><td>1</td><td>100</td></tr> <tr><td>2</td><td>43</td></tr> <tr><td>3</td><td>34</td></tr> <tr><td>4</td><td>15</td></tr> <tr><td>5</td><td>14</td></tr> <tr><td>6</td><td>12</td></tr> <tr><td>7</td><td>7</td></tr> <tr><td>8</td><td>5</td></tr> <tr><td>9</td><td>2</td></tr> <tr><td>10</td><td>2</td></tr> </tbody> </table>	Number of faults	Mitigated faults (%)	1	100	2	43	3	34	4	15	5	14	6	12	7	7	8	5	9	2	10	2
Number of faults	Mitigated faults (%)																						
1	100																						
2	43																						
3	34																						
4	15																						
5	14																						
6	12																						
7	7																						
8	5																						
9	2																						
10	2																						
not_2bit	<p data-bbox="746 853 1158 875">Fault injection study on 'not_2bit', protected voter</p>  <table border="1" data-bbox="587 875 1259 1368"> <thead> <tr> <th>Number of faults</th> <th>Mitigated faults (%)</th> </tr> </thead> <tbody> <tr><td>1</td><td>100</td></tr> <tr><td>2</td><td>64</td></tr> <tr><td>3</td><td>39</td></tr> <tr><td>4</td><td>20</td></tr> <tr><td>5</td><td>9</td></tr> <tr><td>6</td><td>10</td></tr> <tr><td>7</td><td>3</td></tr> <tr><td>8</td><td>2</td></tr> <tr><td>9</td><td>3</td></tr> <tr><td>10</td><td>1</td></tr> </tbody> </table>	Number of faults	Mitigated faults (%)	1	100	2	64	3	39	4	20	5	9	6	10	7	3	8	2	9	3	10	1
Number of faults	Mitigated faults (%)																						
1	100																						
2	64																						
3	39																						
4	20																						
5	9																						
6	10																						
7	3																						
8	2																						
9	3																						
10	1																						
not_32bit	<p data-bbox="746 1413 1158 1435">Fault injection study on 'not_32bit', protected voter</p>  <table border="1" data-bbox="587 1435 1259 1928"> <thead> <tr> <th>Number of faults</th> <th>Mitigated faults (%)</th> </tr> </thead> <tbody> <tr><td>1</td><td>100</td></tr> <tr><td>2</td><td>99</td></tr> <tr><td>3</td><td>95</td></tr> <tr><td>4</td><td>85</td></tr> <tr><td>5</td><td>85</td></tr> <tr><td>6</td><td>76</td></tr> <tr><td>7</td><td>74</td></tr> <tr><td>8</td><td>60</td></tr> <tr><td>9</td><td>52</td></tr> <tr><td>10</td><td>38</td></tr> </tbody> </table>	Number of faults	Mitigated faults (%)	1	100	2	99	3	95	4	85	5	85	6	76	7	74	8	60	9	52	10	38
Number of faults	Mitigated faults (%)																						
1	100																						
2	99																						
3	95																						
4	85																						
5	85																						
6	76																						
7	74																						
8	60																						
9	52																						
10	38																						



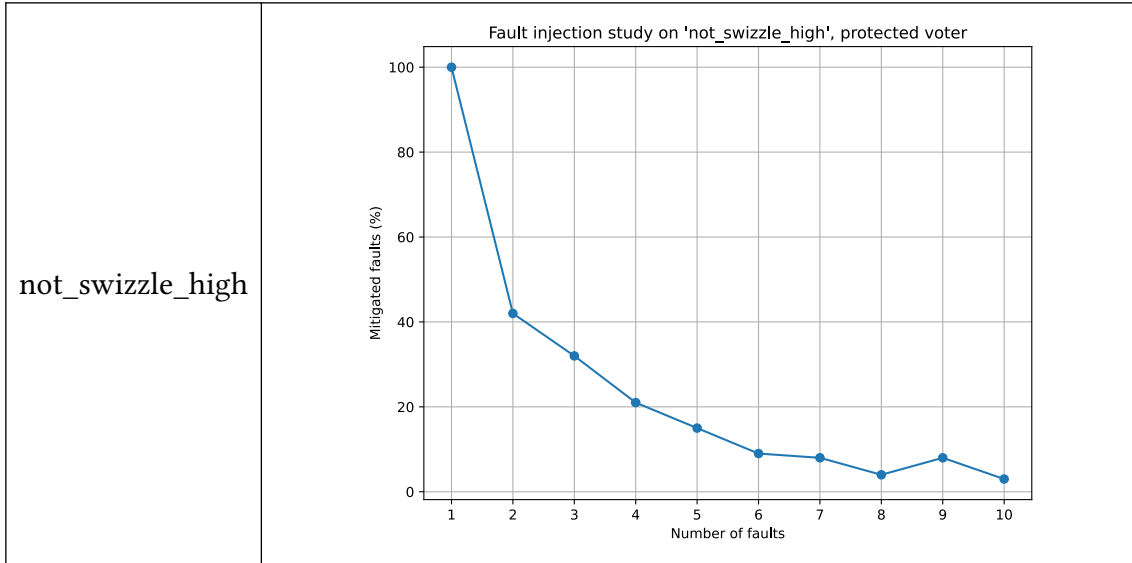
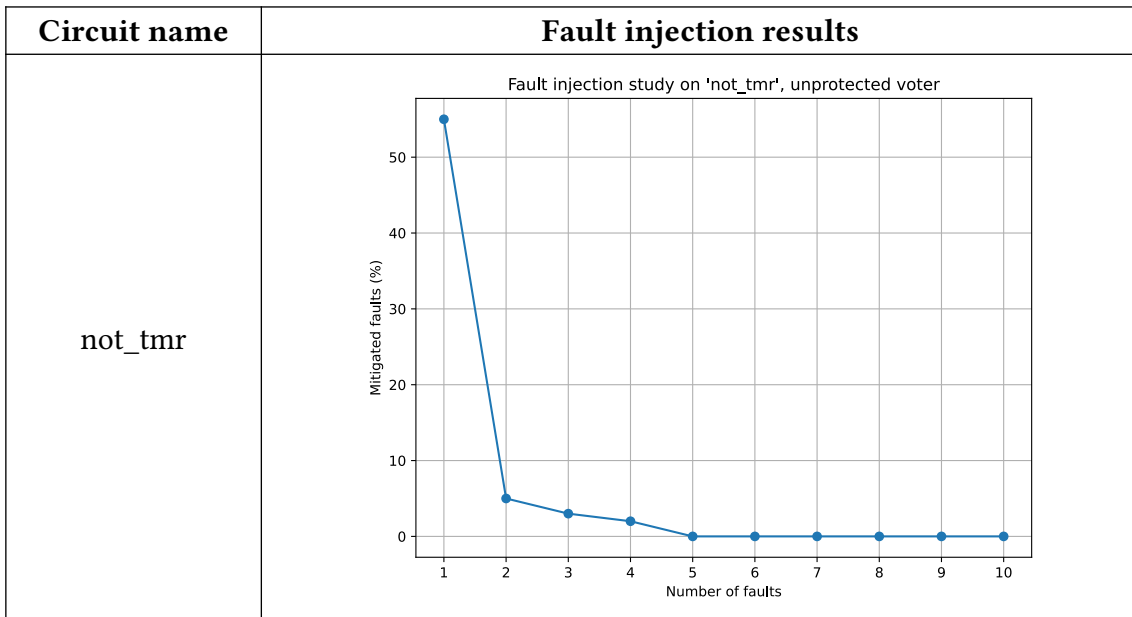


Table 7: Protected voter fault injection study results

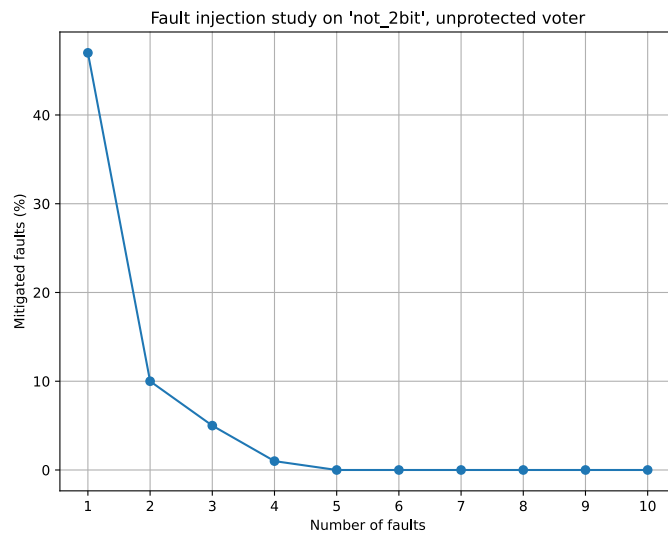
4.2.4. Fault injection studies: Unprotected voter

While the protected voter study in the prior section is useful for verifying the correctness of the voter circuit itself, it is not representative of real-world fault scenarios. In the unprotected voter studies, we subject the entire netlist to faults, including the voter circuit.

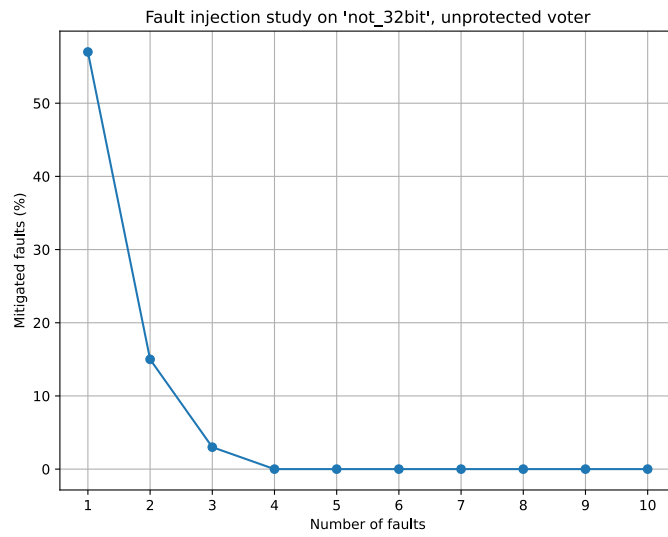
The Yosys script used to run these tests was the same as [Listing 4](#), except that the statements to select only voters were removed. Results for this set of tests are shown in [Table 8](#). The process remains stochastic, and the same parameters as in the protected voter experiments were used (10 samples per fault).



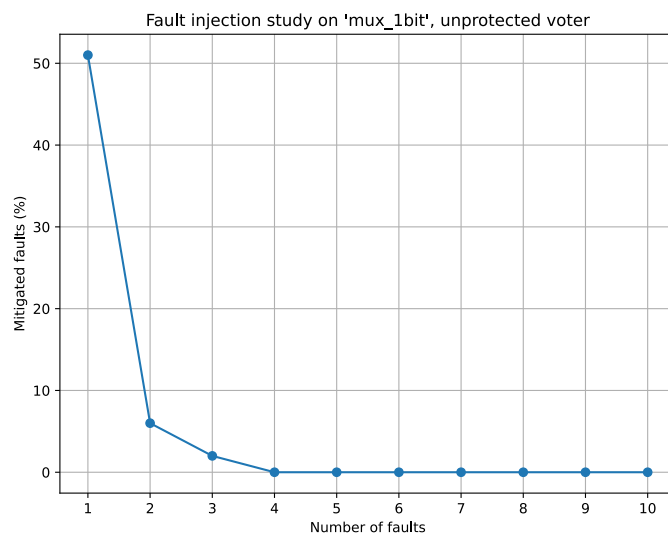
not_2bit



not_32bit



mux_1bit



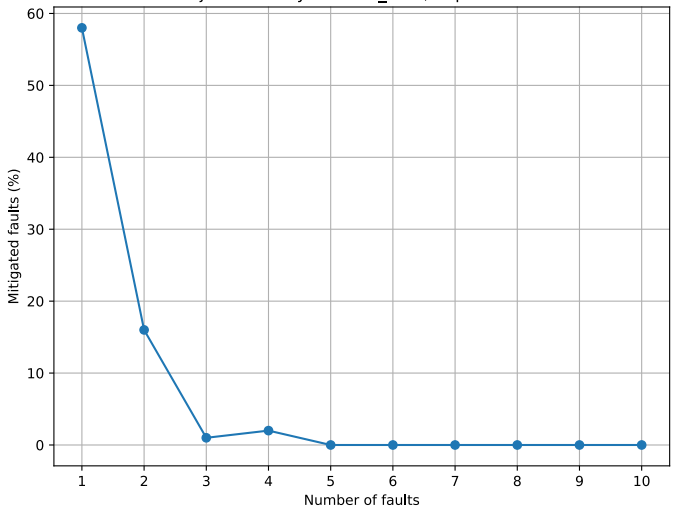
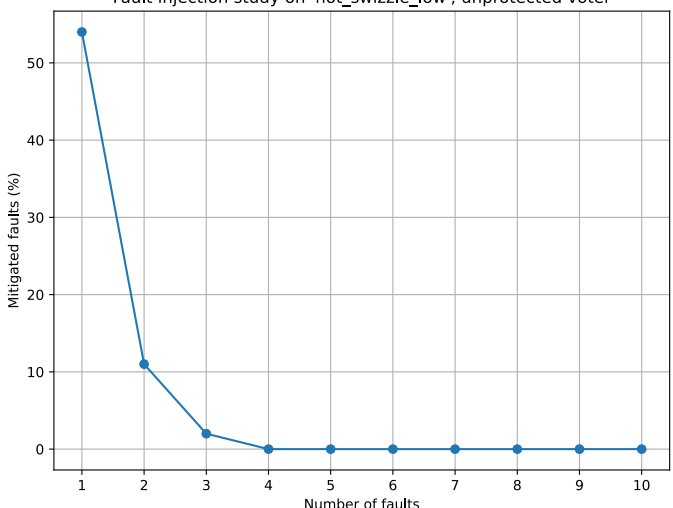
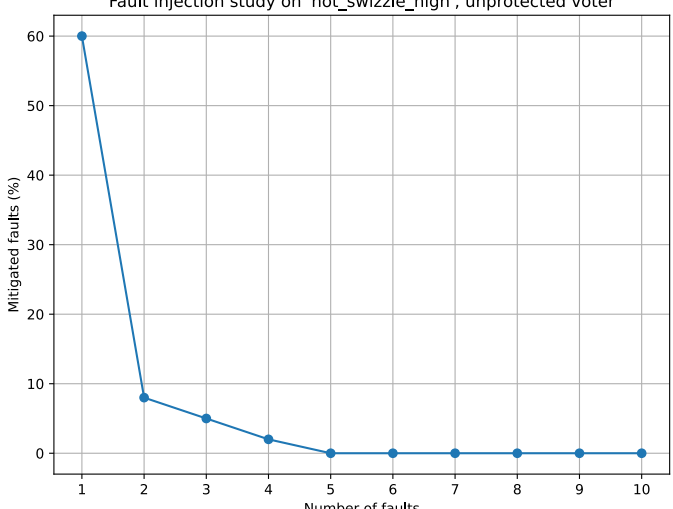
mux_2bit	<p>Fault injection study on 'mux_2bit', unprotected voter</p>  <table border="1"> <thead> <tr> <th>Number of faults</th> <th>Mitigated faults (%)</th> </tr> </thead> <tbody> <tr><td>1</td><td>58</td></tr> <tr><td>2</td><td>16</td></tr> <tr><td>3</td><td>1</td></tr> <tr><td>4</td><td>2</td></tr> <tr><td>5</td><td>0</td></tr> <tr><td>6</td><td>0</td></tr> <tr><td>7</td><td>0</td></tr> <tr><td>8</td><td>0</td></tr> <tr><td>9</td><td>0</td></tr> <tr><td>10</td><td>0</td></tr> </tbody> </table>	Number of faults	Mitigated faults (%)	1	58	2	16	3	1	4	2	5	0	6	0	7	0	8	0	9	0	10	0
Number of faults	Mitigated faults (%)																						
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10	0																						
not_swizzle_low	<p>Fault injection study on 'not_swizzle_low', unprotected voter</p>  <table border="1"> <thead> <tr> <th>Number of faults</th> <th>Mitigated faults (%)</th> </tr> </thead> <tbody> <tr><td>1</td><td>54</td></tr> <tr><td>2</td><td>11</td></tr> <tr><td>3</td><td>2</td></tr> <tr><td>4</td><td>0</td></tr> <tr><td>5</td><td>0</td></tr> <tr><td>6</td><td>0</td></tr> <tr><td>7</td><td>0</td></tr> <tr><td>8</td><td>0</td></tr> <tr><td>9</td><td>0</td></tr> <tr><td>10</td><td>0</td></tr> </tbody> </table>	Number of faults	Mitigated faults (%)	1	54	2	11	3	2	4	0	5	0	6	0	7	0	8	0	9	0	10	0
Number of faults	Mitigated faults (%)																						
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not_swizzle_high	<p>Fault injection study on 'not_swizzle_high', unprotected voter</p>  <table border="1"> <thead> <tr> <th>Number of faults</th> <th>Mitigated faults (%)</th> </tr> </thead> <tbody> <tr><td>1</td><td>60</td></tr> <tr><td>2</td><td>8</td></tr> <tr><td>3</td><td>5</td></tr> <tr><td>4</td><td>2</td></tr> <tr><td>5</td><td>0</td></tr> <tr><td>6</td><td>0</td></tr> <tr><td>7</td><td>0</td></tr> <tr><td>8</td><td>0</td></tr> <tr><td>9</td><td>0</td></tr> <tr><td>10</td><td>0</td></tr> </tbody> </table>	Number of faults	Mitigated faults (%)	1	60	2	8	3	5	4	2	5	0	6	0	7	0	8	0	9	0	10	0
Number of faults	Mitigated faults (%)																						
1	60																						
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10	0																						

Table 8: Unprotected voter fault injection study results

In many of these examples, the results are significantly worse than with the protected voter. This is because the voter takes up the majority of the gate-area of the circuit in a number of these cases, meaning the likelihood of the fault applying to the voter and hence invalidating it is much higher. In Table 9, I calculate the percentage area that the voter accounts for.

Circuit name	Area taken by voter
not_2bit	90.4%
not_32bit	99.3%

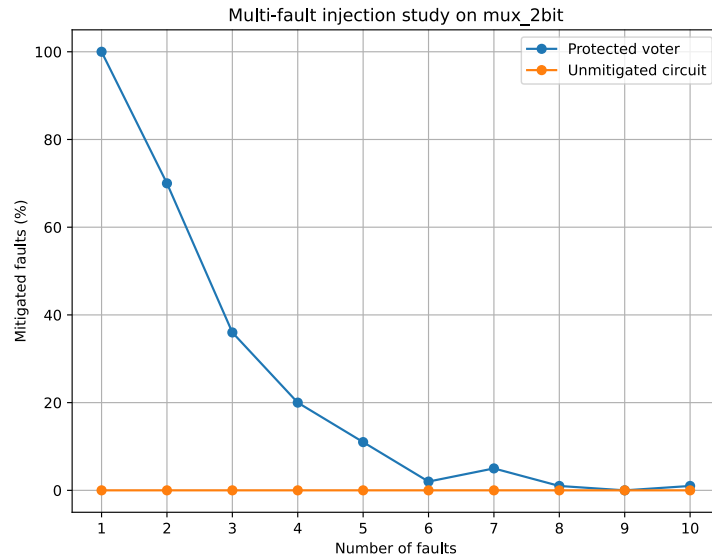
Table 9: Voter area for different circuits

This raises an interesting question for further research. There is an implication here that the area a voter takes up is a very important characteristic that impacts how fault-tolerant a TMR circuit is. This, in turn, suggests that area driven (or, alternatively, placement-driven) TMR approaches would be a valuable field to investigate in future research. Regardless, since TaMaRa operates entirely in the synthesis phase without any knowledge or consideration of the final area the voter takes, it makes sense that high voter areas as per Table 9 correspond with significantly reduced fault-tolerance in unprotected voter scenarios.

4.2.5. Analysis of fault injection results

Synthesising the data from all of the prior tests, we can reveal some interesting properties of the TaMaRa algorithm and the characteristics of its robustness against SEUs.

Firstly, comparing unprotected⁴ vs. unmitigated⁵ circuits for a variety of circuits shows that the TaMaRa algorithm is effective, compared to a control, against mitigating a number of SEUs.



⁴In which the voter is allowed to have faults injected into it.

⁵In which there is no TaMaRa TMR applied at all.

Figure 12: Unmitigated vs. protected voter for the mux_2bit circuit

The fact that 100% of faults are mitigated when only one fault is injected is a positive sign, as it indicates the algorithm is working as intended to mitigate *single* event upsets.

4.3. RTL fuzzing

- Unsure how to show this systematically either

Chapter 5

Conclusion

5.1. Future work

Throughout the duration of this thesis, there have been a number of improvements and areas for future research identified.

Firstly, in future work, it would be very important to address a number of limitations in the TaMaRa algorithm. At this point, the algorithm is unfortunately unable to handle a number of critical circuits, particularly circuits types that are commonly used in industry designs. This includes many (but not all) circuits which use sequential elements such as DFFs, recurrent circuits, and a small number of combinatorial circuits with very complex bit swizzling. The critical flaw that causes this is the lack of robustness of the wiring stage ([Chapter 3.2.6](#) and [Chapter 3.2.7](#)). As an abstraction over any and all circuits at various levels of the design process, RTLIL is extremely complex, and hence splicing an RTLIL netlist to insert majority voters in all of these cases is very challenging. **TODO more on this**

Likewise, there are some limitations in the verification methodology that need to be addressed. Whilst I do believe that the verification proofs are strong for the circuits we were able to prove, there are a number of circuits that I was unable to prove. Particularly, this includes circuits that use sequential logic elements, particularly DFFs. The issue is an unexpected result when injecting numerous faults into the circuit. As shown in Figure XX, after a certain number of faults, even an unmitigated circuit (without any TMR at all!) is apparently able to mitigate 100% of faults. This is a result that should not be possible, and is likely a methodological error caused by the sheer number of faults being introduced into a small circuit being cancelling each other out. **TODO but we can't do more complicated circuits**

TODO solution to L21 method.typ

Appendix A Source code

Source code for the TaMaRa algorithm is available free of charge and under an open-source licence on GitHub: <https://github.com/mattyoun101/tamara>

This repository contains documentation on how to install, configure and process your own circuits using the TaMaRa algorithm.

All TaMaRa code is available under the Mozilla Public License v2.0, a weak copyleft licence. This thesis and all documentation is available under the CC-BY (Creative Commons Attribution) licence.

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