

Efficient Deep Learning for Massive MIMO Channel State Estimation

PhD Thesis (draft)

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Abstract

Future wireless communications networks will rely heavily on massive MIMO technologies where a base station (BS) with large multiantenna arrays serve a large number of user equipment (UE) terminals. Such multiantenna arrays enable high capacity communications via beamforming, as evidenced by work in information theory [1]. To achieve capacity in massive MIMO networks, the base station requires accurate estimates of the channel state information (CSI) in order to precode (decode) transmitted (received) messages [2].

CSI can be acquired using pilot signals, and in time-division duplex (TDD) mode, channel reciprocity allows the BS to estimate the downlink CSI via pilots in uplink transmissions. However, in frequency division duplex (FDD) mode, channel reciprocity between uplink and downlink channels is weak, and the BS must rely on feedback from the UE to estimate downlink CSI. Specifying an appropriate CSI feedback scheme is a key issue and involves a reducing feedback bandwidth while maintaining accurate downlink CSI estimates.

Conventional methods for CSI feedback compression typically rely on compressed sensing (CS), which seeks to reconstruct high-dimensional data based on low-dimensional measurements (see [3] for a survey of CS methods). Many CS methods rely on convex relaxations of an underdetermined least-squares problem, and such methods rely on iterative solvers (e.g., the proximal gradient method). When using an iterative solver, reconstruction can consume an undue amount of time even when measurements are available, making faster methods for reconstruction desirable.

Recent work in deep learning for compressed CSI estimation has presented viable alternatives to CS methods [4]. Such work typically employs convolutional neural networks (CNNs) to learn compressed representations of high-dimensional CSI, and the architectures

used in CNN-based works can be placed in one of two categories. The first category, CNN-based autoencoders, consists of networks which utilize two subnetworks: an encoder network which learns a low-dimensional representation with the original data as an input and a decoder network which estimates the original data as a function of the low-dimensional representation. The second category, unrolled optimization networks, draws inspiration from the aforementioned CS methods by structuring the CNN as a finite number of repeated blocks, each of which imitates an iteration of a given CS algorithm.

This thesis explores both CNN autoencoders and unrolled optimization networks for CSI estimation while focusing domain knowledge to improve the performance of these CSI estimation networks with respect to accuracy, feedback rate, or network efficiency. Prior works have demonstrated superior performance over these architectures over conventional CS methods [4, 5], and this thesis investigates the myriad ways that domain knowledge in wireless channels and communications protocols can be leveraged to improve CSI estimation.

Chapter 1

Introduction

This dissertation details work in improving the accuracy and efficiency of deep learning methods for MIMO channel state information estimation. This chapter provides the necessary background to understand the contributions of the dissertation. Section 1.1 provides an overview of the MIMO channel and the importance of CSI estimation in MIMO-based communications networks. Section 1.3 discusses MIMO channel models and introduces the primary channel model used in this work, the COST2100 model. Section 1.4 discusses prior work in compressed sensing for CSI estimation. Section 1.5 provides a generic overview of deep learning. Boldface lowercase (uppercase) letters indicate vectors (matrices). Unless otherwise specified, the norm $\|\cdot\|$ indicates the Frobenius norm. Superscripts T (H) indicate the transpose (Hermitian transpose).

1.1 MIMO Channel Overview

In this work, we consider a MIMO channel with a multiple antennas ($N_B \gg 1$) at the transmitter (gNodeB or gNB) servicing a single user equipment (UE) with a single antenna. Under orthogonal frequency division multiplexing (OFDM) with N_f subcarriers, the received symbols on the m -th subcarrier for the downlink and the uplink at the receiver are



Figure 1.1: Example multi-antenna transmitter (BS, gNB) and single-antenna user equipment (UE) and relevant system values.

Table 1.1: MIMO system variables considered in this work.

Symbol	Dimension	Description
$y_{d,m}$	\mathbb{C}^1	Received downlink symbol on m -th subcarrier
$\mathbf{h}_{d,m}$	$\mathbb{C}^{N_b \times 1}$	Downlink channel on m -th subcarrier
$\bar{\mathbf{H}}_d$	$\mathbb{C}^{N_f \times N_b}$	Downlink CSI (spatial-frequency domain)
$\mathbf{w}_{t,m}$	$\mathbb{C}^{N_b \times 1}$	Transmitter precoding vector for m -th subcarrier
$x_{d,m}$	\mathbb{C}^1	Transmitted symbol on m -th subcarrier
$n_{d,m}$	\mathbb{C}^1	Downlink noise on m -th subcarrier
$\tilde{\mathbf{H}}_d$	$\mathbb{C}^{N_f \times N_b}$	Downlink CSI (angular-delay domain)
\mathbf{H}_d	$\mathbb{C}^{R_d \times N_b}$	Truncated downlink CSI (angular-delay domain)

given as

$$y_{d,m} = \mathbf{h}_{d,m}^H \mathbf{w}_{t,m} x_{d,m} + n_{d,m}.$$

where the individual system values are defined in Table 1.1, and a representative system model is viewable in Figure 1.1. The resulting downlink and uplink channel state information (CSI) matrices are given as

$$\bar{\mathbf{H}}_d = \begin{bmatrix} \mathbf{h}_{d,1} & \dots & \mathbf{h}_{d,N_f} \end{bmatrix}^H \in \mathbb{C}^{N_f \times N_b}.$$

To achieve near-capacity transmission rates, the transmitter needs access to an appropriate estimate of $\bar{\mathbf{H}}_d$ [1]. Such estimates enable the use of linear precoding techniques (e.g., con-

jugate beamforming or zero-forcing beamforming) to realize appreciable spectral and power efficiency gains [6]. Downlink CSI estimation can be performed in time division duplex (TDD) by using uplink pilots due to channel reciprocity [7–9]. In contrast, frequency division duplex (FDD) does not admit channel reciprocity due to frequency-selective channels, meaning CSI estimates must be acquired at the UE using pilot signals, and these estimates must be compressed then fed back to the BS.

1.2 Practical Pilot-based Channel Estimation in 4G/5G Networks

To estimate the downlink CSI in wireless networks, transmitters allocate pilot reference signals. To reserve spectral resources, pilots are restricted to a limited number of spatial-frequency positions, and the allocation of these pilots is defined in the 3GPP technical standards, TS 36.211 for 4G/LTE networks [10] and TS 38.211 for 5G/NR networks [11]. In these two standards, the pilots are called CSI reference signals (CSI-RS) or demodulation reference signals (DM-RS), respectively. Figure 1.2 shows valid placements of CSI-RS/DM-RS in the time-frequency resource grid as defined by TS 36.211 and TS 38.211.

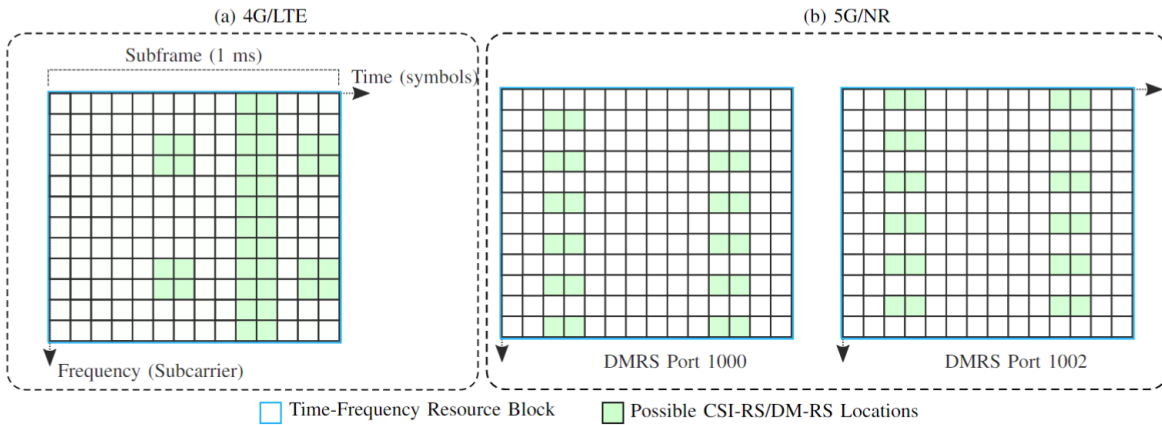


Figure 1.2: (a) LTE resource blocks with CSI-RS locations. (b) 5G NR resource blocks with DM-RS locations.

While many using deep learning for CSI estimation do not address pilot estimation ex-

plicitly, a few works have incorporated pilot estimation into the CSI feedback problem.

1.3 Geometric Stochastic Channel Models (GSCMs)

Ideally, the datasets used for the CSI estimation task would be derived from measurement campaigns (e.g., see [12–14]). However, the financial and labor costs of acquiring these datasets can be prohibitive in certain situations. In such situations, researchers rely on geometric stochastic channel models (GSCMs), models which are so called since they consider the **geometry** of scatterers in the wireless environment and the **stochastic** nature of the channel. Simulations based on GSCMs are advantageous to researchers for a few reasons:

- (1) Simulations permit the generation a large quantities of data in a (relatively) short period of time.
- (2) Simulations enable the adjustment of parameters of the communications system (e.g., carrier frequency, UE mobility, subcarrier spacing).

GSCMs consider the problem of modeling the wireless channels at two different scales. At a small-scale, the focus is on the modeling of “scatterers,” objects in the environment which reflect the electromagnetic waves transmitted during. Examples of scatterers in an outdoor environment are buildings, balconies, cars, and trees, while examples of scatters in an indoor environment are walls, furniture, and people. Due to the presence of many scatterers, electromagnetic waves transmitted from a BS arrive at UEs along multiple paths at different delays, and accordingly, the scatterers are often referred to as **multipath components (MPCs)**. From the UE’s perspective, the MPCs are often grouped together in specific delay regions, and each such grouping of MPCs is referred to as a **cluster**.

While the modeling of MPCs and clusters is vital, also vital is ensuring that the results of the GSCM-based simulations are statistically consistent with the measured channel data.

Table 1.2: Parameters used for COST2100 simulations for both Indoor and Outdoor datasets.

Symbol	Value	Description
N_b	32	Number of antennas at gNB
N_f	1024	Number of subcarriers for OFDM link
R_d	32	Number of delay elements kept after truncation
N	10^6	Total number of samples per dataset
T	10	Number of timeslots
δ	40 ms	Feedback delay interval between consecutive CSI timeslots

For all CSI tests, we mainly rely on the COST2100 MIMO channel model [15]. We use two datasets with a single base station (gNB) and a single user equipment (UE) in the following scenarios:

- (1) **Indoor** channels using a 5.3GHz downlink at 0.001 m/s UE velocity, served by a gNB at center of a $20\text{m} \times 20\text{m}$ coverage area.
- (2) **Outdoor** channels using a 300MHz downlink at 0.9 m/s UE velocity served by a gNB at center of a $400\text{m} \times 400\text{m}$ coverage area.

In both scenarios, we use the parameters listed in Table 1.2.

1.4 Classical CSI Estimation

Works in compressive feedback for CSI estimation in MIMO networks can be placed in three broad categories. The first category includes works which use direct quantization of continuous CSI elements to discrete levels. The quantized CSI are encoded and fed back to the transmitter [16, 17]. The second category includes works which use compressed sensing, a technique which applies a random measurement matrix at the transmitter and the receiver [18, 19]. Compressed sensing assumes matrices to be encoded and fed back meet certain sparsity requirements, and compressed sensing algorithms require iterative solvers [20] for decoding, resulting in undesired latency.

The last category of work in compressive CSI feedback uses deep learning (DL), neural networks with numerous layers which are trained on large datasets using backpropagation. Before describing these works, we first describe a few pertinent concepts from deep learning.

1.5 Deep Learning Background

This section provides a brief overview of relevant deep learning concepts employed in this work, including convolutional neural networks (CNNs), autoencoders, and unsupervised learning.

Deep learning (DL) is a subset of machine learning (ML), a broad class of algorithms which use data to “fit” models for prediction or classification tasks. The three predominant learning frameworks are supervised learning, unsupervised learning, and reinforcement learning. In the works proposed, we focus on *unsupervised learning*, which seeks to find a compressed representation of the data without labels (see Chapter 14 of [21] for an overview).

Convolutional Neural Networks: A neural network is a machine learning algorithm with multiple *layers* of parameterized linear functions followed nonlinear functions (typically referred to as ‘activation’ functions). The parameters for these layers can be updated via a stochastic optimizer (e.g., [22]), and given enough layers, such networks can achieve arbitrarily accurate functional approximation [23]. In recent years, neural networks with convolutional layers have established state-of-the-art performance in computer vision tasks such as image classification [24] and segmentation [25].

A common architecture for deep unsupervised learning is the *autoencoder* (see Fig. 1.3 for a generic example). Trained end-to-end on input data, an autoencoder is comprised of an encoder and a decoder which jointly learn a compressed latent representation (\mathbf{Z}) and an estimate of the input ($\hat{\mathbf{H}}$). By choosing \mathbf{Z} to have lower dimension than the input, the network is forced to learn a “useful” summary of the input data. The typical objective function for

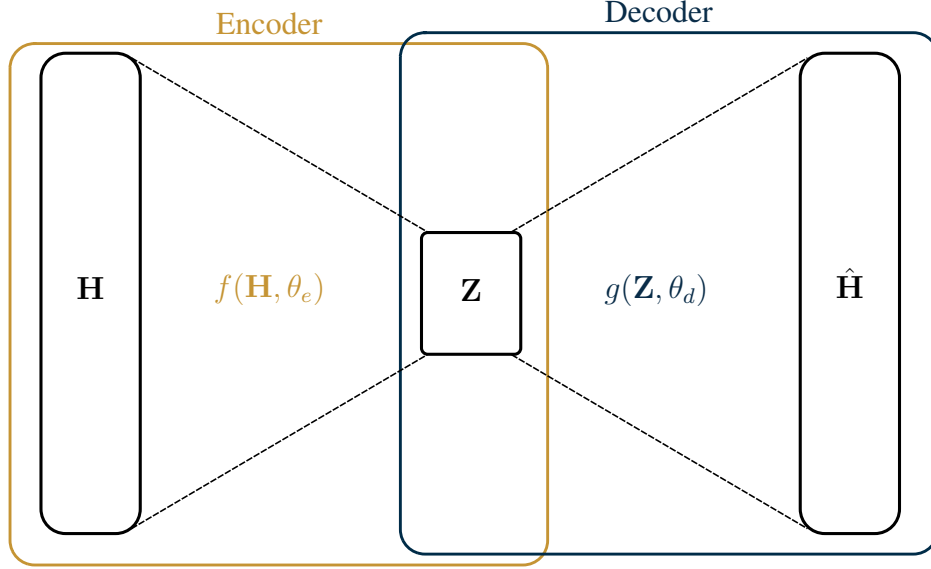


Figure 1.3: Abstract schematic for an autoencoder operating on CSI matrices \mathbf{H} . The encoder learns a latent representation, \mathbf{Z} , while the decoder learns to reconstruct estimates $\hat{\mathbf{H}}$.

such a network is the mean squared error (MSE),

$$\operatorname{argmin}_{\theta_e, \theta_d} \frac{1}{N} \sum_{i=1}^N \|\mathbf{H}_i - g(f(\mathbf{H}_i, \theta_e), \theta_d)\|^2.$$

We optimize network parameters $\vec{\theta}_e, \vec{\theta}_d$ by backpropagation and a stochastic optimization algorithm (e.g., stochastic gradient descent, ADAM).

1.6 Objective and Contributions

Successful efforts in DL for CSI estimation have typically utilized convolutional neural networks (CNNs) in an autoencoder structure [4]. Variations on the CNN-based autoencoder have investigated different network architectures [26], variational training frameworks [27], and denoising modules [28]. These architectural changes are largely inspired by successful application of DL in image compression [29–31].

While they can continue to push the state-of-the-art in CSI reconstruction accuracy, architectural optimizations may ultimately follow the same trends of fields such as language

modeling, where state-of-the-art performance requires prohibitively massive compute [32]. In this proposal, we take a different approach seek to improving compressive channel feedback by focusing on domain knowledge and physical insight.

This qualifying exam proposal details our attempts to use domain knowledge to enhance the performance and the efficiency of neural networks for CSI estimation (for a visual summary, see Figure 1.4). Section 2 details our work in power-based normalization, which leverages CSI sparsity. Section 3 describes our work in differential encoding, which exploits temporal coherence of CSI. Section 4 describes our work in pilot-based delay domain CSI estimation.

Figure 1.4: Venn diagram highlighting different aspects of domain knowledge in CNN-based CSI compressive feedback, relevant convolutional networks, and our contributions.

Chapter 2

Data Pre-processing and Normalization

In this chapter, we will discuss the data pre-processing techniques and the applications of domain knowledge that have enabled successful application of deep learning to MIMO CSI estimation (Section 2.1), including our proposed pre-processing technique, spherical normalization (Section 2.3).

2.1 Data Pre-processing for CSI Data

The success of machine learning tasks relies on proper *data pre-processing*, a sequence of transformations used on the input data before fitting a model. In any machine learning task, data pre-processing is necessary to ensure that the scales of input features are similar. In deep learning, three important pre-processing techniques are domain transformations, truncation, or normalization, and here we will explore the choices in pre-processing that different authors have made based on domain knowledge of MIMO CSI data.

2.1.1 Sparse Basis for CSI

The first type of data pre-processing we consider is a domain transformation, the discrete Fourier transform in particular. While the **spatial-frequency** representation $\bar{\mathbf{H}}$ is used for

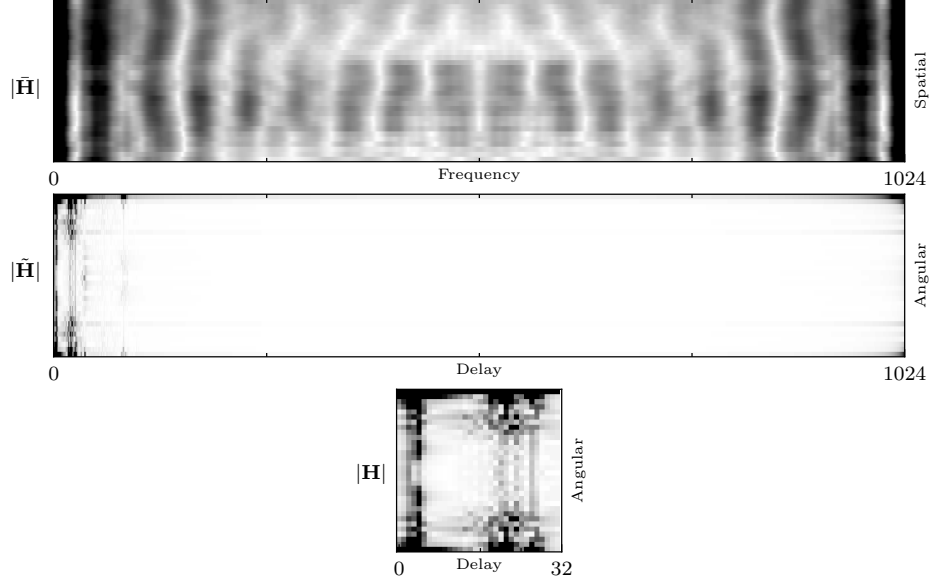


Figure 2.1: Magnitude of spatial-frequency ($\tilde{\mathbf{H}}$), angular-delay ($\tilde{\mathbf{H}}$), and truncated angular-delay (\mathbf{H}) representations for a single random channel from the outdoor COST2100 dataset.

beamforming at the transmitter, the number of non-zero elements is comparatively large. Given the dimension of $\tilde{\mathbf{H}}$, feeding back entire CSI matrices is impractical. Instead, we seek a compressed representation of a sparse transformation. The sparse representation we consider is the angular-delay representation of CSI matrices [33]. Denote the unitary inverse DFT for the spatial (frequency) axis as $\mathbf{F}_a \in \mathbb{C}^{N_b \times N_b}$ ($\mathbf{F}_d^H \in \mathbb{C}^{N_f \times N_f}$), and denote the spatial-frequency CSI matrix as $\tilde{\mathbf{H}}$. The angular-delay domain representation $\tilde{\mathbf{H}}$ is given as

$$\tilde{\mathbf{H}} = \mathbf{F}_d^H \tilde{\mathbf{H}} \mathbf{F}_a.$$

The delay spread of the resulting $\tilde{\mathbf{H}}$ can typically be captured with a small number of delay elements (see Figure 2.2), so we restrict our attention to the first R_d elements of $\tilde{\mathbf{H}}$, resulting in a truncated angular-delay matrix which we denote as $\mathbf{H} \in \mathbb{C}^{(R_d \times N_b)}$ for the downlink channel state. An illustrative example of this truncation can be seen at the bottom of Figure 2.1.

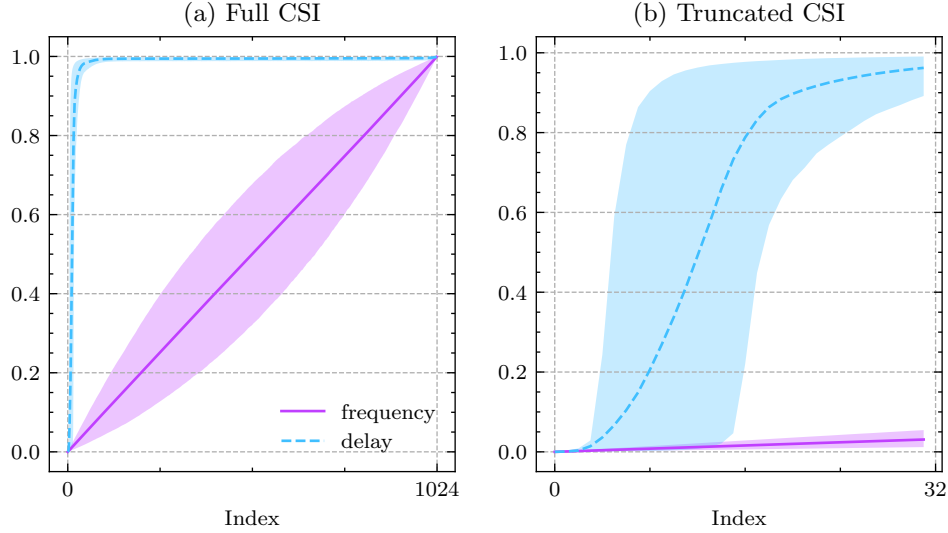


Figure 2.2: Energy CDF for 5000 CSI samples of 32 antennas and 1024 subcarriers, generated from COST2100 outdoor models described in Section 1.3. Mean percentage of energy in CSI matrix up to index is shown with 90% confidence intervals. The index denotes the amount of energy accounted for up to the corresponding frequency/delay element. The truncated angular-delay CSI contains a mean energy of 96.2% (c.i. 89.2%, 99.1%), while the truncated frequency-spatial CSI only contains a mean energy of 3.1% (c.i. 1.2%, 5.4%).

2.1.2 Bidirectional Reciprocity in FDD Networks

The next type of pre-processing under consideration is a change of coordinates. Specifically, rather than utilizing a Cartesian representation (i.e., real-imaginary channels), we can consider a polar representation (i.e., magnitude-phase). As discussed in Section 1.1, the reciprocity of downlink and uplink channels is weak in FDD wireless networks when compared to TDD. Despite this, DL CSI estimation techniques have used uplink CSI to improve the reconstruction accuracy of downlink CSI at gNB. In [34], the authors demonstrate that the correlation between the magnitude of uplink and downlink CSI elements is strong. To exploit magnitude reciprocity, they propose DualNet, a CNN autoencoder which learns a feedback encoding for the downlink CSI magnitude and decodes the feedback with the magnitude of uplink CSI as side information. The downlink phase is separately quantized and fed back to gNB via magnitude-dependent phase quantization (MDPQ). The authors demonstrate that exploiting bidirectional reciprocity can substantially improve CSI estimation accuracy.

2.1.3 Minmax Normalization

The last pre-processing technique we discuss is normalization. Typical deep autoencoders require normalized data to ensure that the range of the input data matches the range of the autoencoder's output function, which is typically chosen as `sigmoid` or `tanh` as pictured in Figure 2.3. To accommodate such output functions, most works in both image

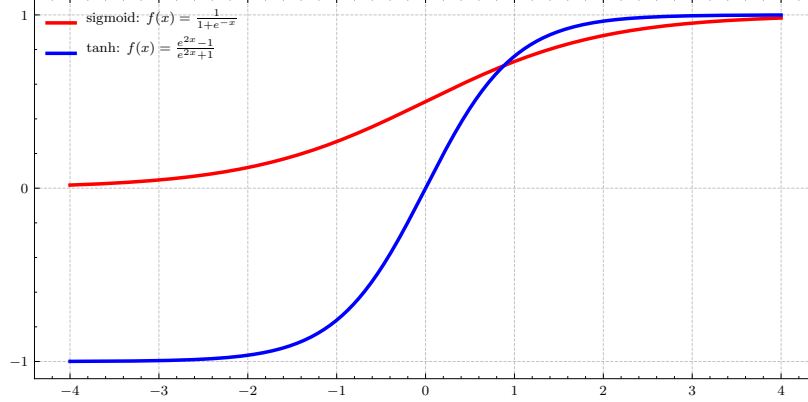


Figure 2.3: Typical activation functions used at the output of convolutional autoencoders.

compression and CSI estimation typically apply *minmax normalization*, where the extrema (i.e., the minimum and the maximum) of the real and imaginary channels are used to scale the entire dataset. For the scalar $H_n(i, j)$, the minmax-scaled version of this element is

$$H_{n,\text{minmax}}(i, j) = \frac{H_n(i, j) - H_{\min}}{H_{\max} - H_{\min}} \in [0, 1],$$

for $n \in [1, \dots, N]$ given a dataset of N samples and i/j indexing the rows/columns of the CSI matrices. The resulting samples are cast to the range $[0, 1]$.

For image data, minmax normalization results in each image's color channels scaled to the range $[0, 1]$. The resulting distribution for each color channel is typically satisfactory for image tasks, as the variance is not much smaller than the range of the normalized data (see Fig. 2.4).

However, for CSI matrices, minmax normalization is applied to the real and imaginary channels of each element. For typical channel models and parameters, the distribution of

channel elements tends to have much lower variance than that of image data (see Fig. 2.5). This smaller variance can be explained by the difference in the datasets’ ranges – while the channels in image data (e.g., ImageNet) assume integer values between $[0, 255]$, the channels in CSI data (e.g., COST2100) assume floating point values smaller than 10^{-3} .

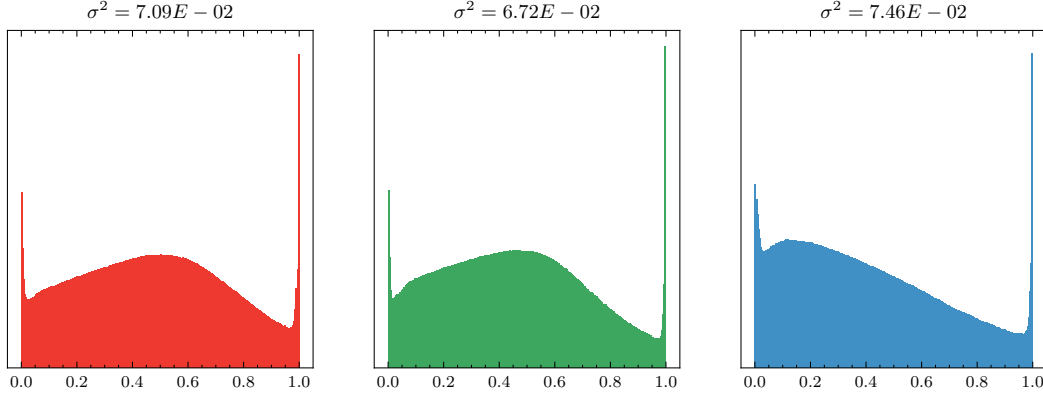


Figure 2.4: Distribution and variance of minmax-normalized ImageNet color channels ($N = 50000$) images.

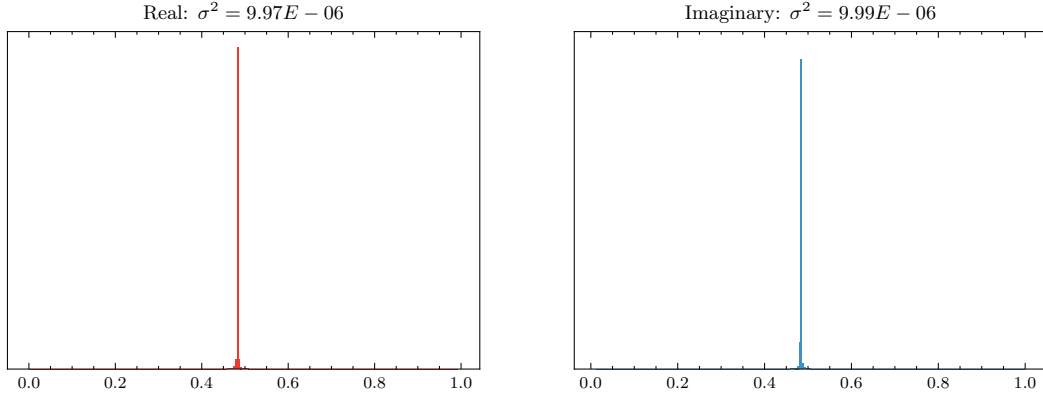


Figure 2.5: Distribution and variance of minmax-normalized COST2100 real/imaginary channels ($N = 99000$) images.

2.2 Related Work

In image processing, several works have investigated normalization techniques such as batch normalization [35], instance normalization [36], layer normalization [37], and group

normalization [38]. These normalization techniques scale the outputs of latent layers in neural networks, which helps to solve the problem of covariate shift [35] where the mean and variance of changes between subsequent layers of the network.

Other works have studied normalization of the network’s inputs. A number of works have investigated adaptive normalization techniques for time series estimation tasks [39–41]. In [42], the authors proposed a trainable input network which learns to shift, scale, and filter the unnormalized data while training the target network for a time series prediction task.

2.3 Spherical Normalization

Here, we discuss our work in spherical normalization (Section 2.3) and our optimized network architecture, CsiNet-Pro (Section 2.3.1) [43].

Rather than apply minmax normalization, which is adversely impacted by outliers, we propose spherical normalization. Before describing spherical normalization in detail, consider z-score normalization. Given a random variable, x , with mean μ and standard deviation σ . The z-score normalized version of this random variable is given as

$$z = \frac{x - \mu}{\sigma^2}. \quad (2.1)$$

Assuming x is normally distributed, the resulting random variable, z , is a standard normal distribution such that $z \sim \mathcal{N}(0, 1)$. Inspired by z -score normalization, we seek a normalization scheme which adjusts the range of each channel sample. Under spherical normalization, each sample in the dataset is scaled by its power. Denote the n -th downlink CSI matrix of the dataset as \mathbf{H}_d^n . The spherically normalized version of the downlink CSI is given as

$$\tilde{\mathbf{H}}_d^n = \frac{\mathbf{H}_d^n}{\|\mathbf{H}_d^n\|}. \quad (2.2)$$

Observe that (2.2) is similar to (2.1) without the mean shift in the numerator¹ and with the power term of each CSI sample rather than the variance of the entire distribution. After applying (2.2) to each sample, minmax scaling is applied to the entire dataset. The resulting dataset under spherical normalization can exhibit a larger variance than the same dataset under minmax scaling (compare Fig. 2.6 with Fig. 2.5).

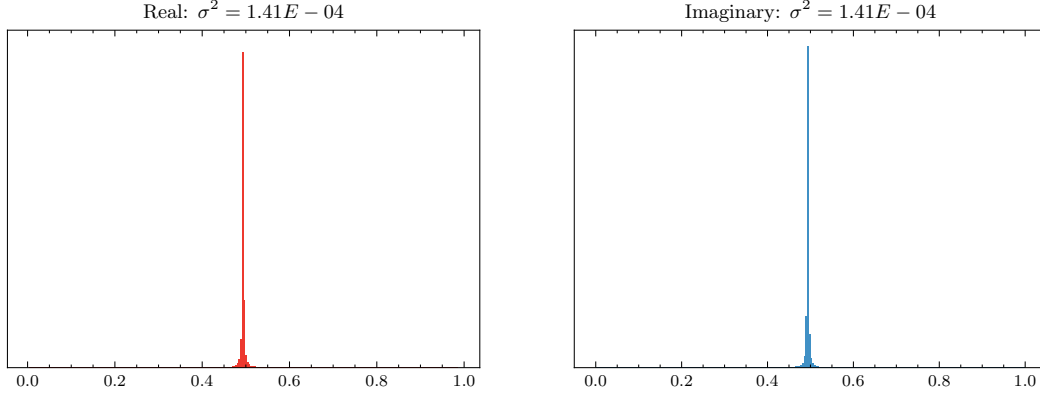


Figure 2.6: Distribution and variance of COST2100 real/imaginary channels under spherical normalization ($N = 99000$) images.

Beyond desirable properties in the input distribution, spherical normalization also results in an objective function which is better matched with the evaluation criterion. Neural networks for CSI estimation are optimized using the mean-squared error loss,

$$\text{MSE} = \frac{1}{N} \sum_{k=1}^N \|\mathbf{H}_k - \hat{\mathbf{H}}_k\|^2, \quad (2.3)$$

while channel state reconstruction accuracy is measured in terms of normalized mean-squared error,

$$\text{NMSE} = \frac{1}{N} \sum_{k=1}^N \frac{\|\mathbf{H}_k - \hat{\mathbf{H}}_k\|^2}{\|\mathbf{H}_k\|^2}. \quad (2.4)$$

¹Since the mean of COST2100 data is $\approx 10^{-10}$, we can safely ignore this mean shift in spherical normalization.

Observe that when the \mathbf{H}_k ($\hat{\mathbf{H}}_k$) in (2.3) is replaced with $\check{\mathbf{H}}_k$ ($\hat{\check{\mathbf{H}}}_k$), we have

$$\begin{aligned} \frac{1}{N} \sum_{k=1}^N \|\check{\mathbf{H}}_k - \hat{\check{\mathbf{H}}}_k\|^2 &= \frac{1}{N} \sum_{k=1}^N \left\| \frac{\mathbf{H}_k}{\|\mathbf{H}_k\|^2} - \frac{\hat{\mathbf{H}}_k}{\|\mathbf{H}_k\|^2} \right\|^2 \\ &= \frac{1}{N} \sum_{k=1}^N \frac{\|\mathbf{H}_k - \hat{\mathbf{H}}_k\|^2}{\|\mathbf{H}_k\|^2}, \end{aligned}$$

which is equivalent to (2.4). Thus, a neural network optimized with MSE as the loss function and trained using spherically normalized data is in fact being optimized with respect to NMSE of the original data.

2.3.1 CsiNet-Pro

In [43], we proposed a network with larger convolutional kernels and no residual connections called CsiNet-Pro. Large kernels (e.g., (7×7) in CsiNet-Pro) allow the network to capture features corresponding to larger delay spreads than comparatively small kernels (e.g., (3×3) in CsiNet [4]). In addition to the compressed feedback of the autoencoder, the encoder must feedback the power of the CSI matrix, $\|\mathbf{H}\|$, meaning the number of floating point elements to feed back increases from r to $r + 1$.

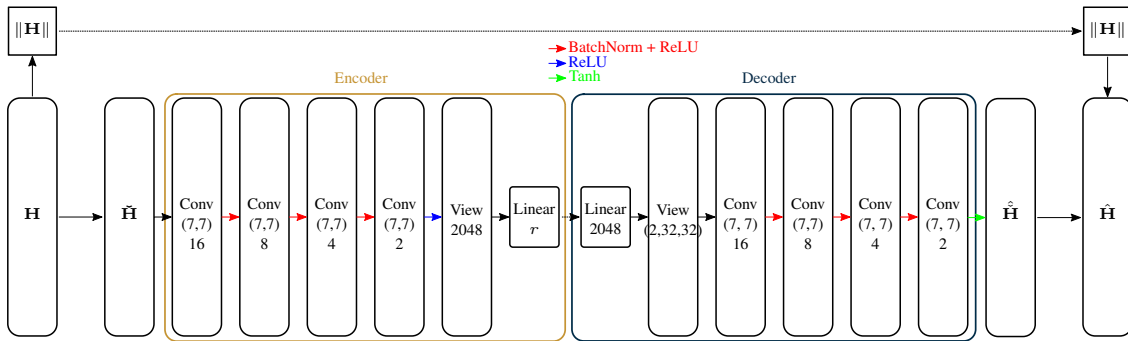


Figure 2.7: SphNet – CsiNet-Pro architecture with Spherical Normalization.

2.3.2 Results

Training on spherically normalized data and optimizing with respect to NMSE can yield better accuracy. Fig. 2.8 demonstrates this improvement for CsiNet and CsiNet-Pro on the COST2100 dataset. CsiNet and CsiNet-Pro are trained with minmax normalization while CsiNet-Sph and SphNet are trained with spherical normalization.

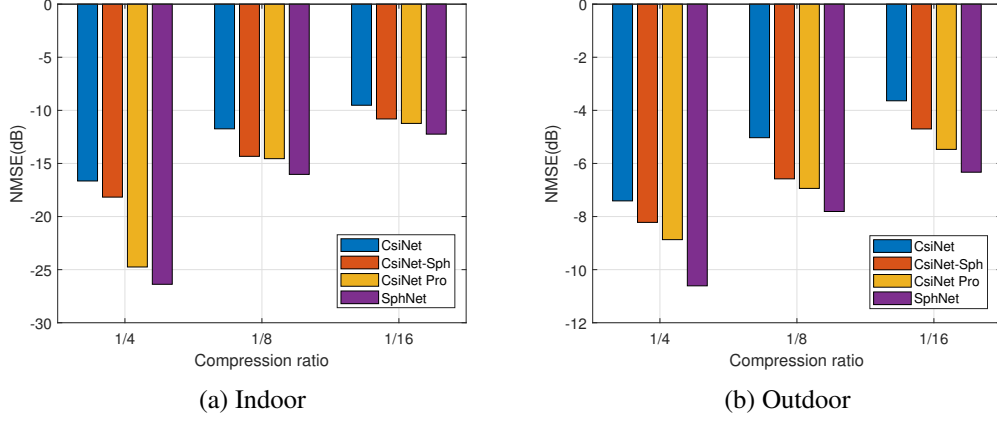


Figure 2.8: Reconstruction error for CsiNet [4] and CsiNet-Pro with and without spherical normalization. SphNet combines CsiNet-Pro with spherical normalization [43].

Chapter 3

Temporal Coherence

In this chapter, we consider methods for exploiting temporal correlation between CSI of subsequent timeslots. The *coherence time* of a channel is the amount of time that a channel estimate can be used before that estimate's SNR falls beneath a given threshold [44]. Within this window of time ($\Delta t = t_i - t_{i-1}$), the correlation between CSI matrices \mathbf{H}_i and \mathbf{H}_{i-1} is high (see Figure 3.1 for an illustrative example).

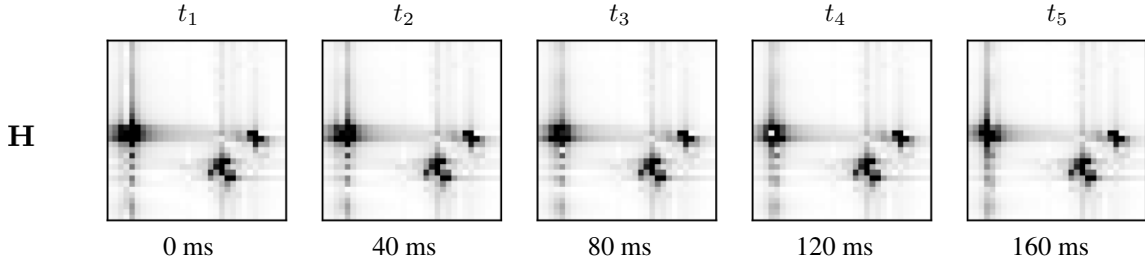


Figure 3.1: Ground truth CSI (\mathbf{H}) for five timeslots (t_1 through t_5) on one sample from the validation set of the outdoor dataset.

Assuming the channel exhibits temporal coherence within a certain window of time, a reasonably accurate CSI estimate at time t_{i-1} can be used to estimate the CSI at time t_i . Generically, we can write this estimator as

$$\hat{\mathbf{H}}_i = h(\hat{\mathbf{H}}_{i-1}) \quad (3.1)$$

where \mathbf{H}_i is the CSI matrix at time t_i and $\hat{\mathbf{H}}_i$ is its estimator. The estimation error under $\hat{\mathbf{H}}_i$ is

$$\mathbf{E}_i = \mathbf{H}_i - \hat{\mathbf{H}}_i. \quad (3.2)$$

3.1 Recurrent Neural Networks

Prior work in temporal correlation for CSI estimation utilized state-space methods such as the Kalman filter [45–47]. Since it relies on explicit state space and noise models, the Kalman filter’s predictive power in CSI estimation is limited. Furthermore, such work generally does not propose a method for feedback compression, making comparison with the following ML methods difficult.

Recent works have leveraged recurrent neural networks (RNNs) to exploit temporal correlation for CSI estimation [48–52]. RNNs include recurrent layers, such as the long short-term memory (LSTM) cell or the gated recurrent unit (GRU), which are capable of learning long-term dependencies of a given process through backpropagation [53] and can be used to predict future states of the process [54].

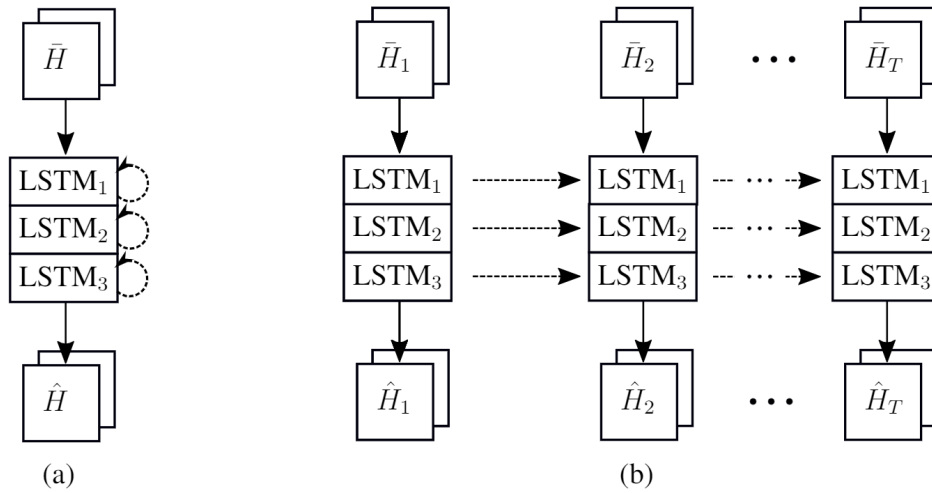


Figure 3.2: An example of LSTMs used for CSI estimation. (a) “Stacked” LSTM network of depth 3 shown with recurrent connections. (b) Same LSTM network “unrolled” into T timeslots

RNNs have been used extensively in natural language processing (NLP) for machine translation [55] and sentiment extraction [56]. For such works in NLP, authors have empirically found “stacked” or “deep” RNNs to be effective (e.g., Fig. 3.2), hypothesizing that having multiple recurrent layers allows the network to extract different semantic timescales [56, 57]. Works in CSI estimation have taken cues from this work in NLP, proposing CSI estimation networks with stacked LSTMs after a sequence of autoencoders [52]. While such work has demonstrated the utility of RNNs, the computational cost of LSTMs can be prohibitively high. For example, the RNN portion of the network proposed in [52] accounts for 10^8 additional parameters. Since channel estimation should not place an undue computational burden on the communications system, LSTMs can be problematic.

3.2 Differential Encoding

Rather than use RNNs to extract temporal dependencies in CSI data, we proposed a lightweight network based on the principle of differential encoding. We trained a network to estimate the error (3.2) under a linear estimator,

$$\hat{\mathbf{H}}_i = \hat{\mathbf{H}}_{i-1} \mathbf{W}$$

where $\mathbf{W} \in \mathbb{C}^{R_b \times R_b}$ is the minimum mean squared error (MMSE) estimator,

$$\begin{aligned} \mathbf{H}_i &= \mathbf{H}_{i-1} \mathbf{W} + \mathbf{E}_i \\ \mathbf{H}_{i-1}^H \mathbf{H}_i &= \mathbf{H}_{i-1}^H \mathbf{H}_{i-1} \mathbf{W} + \underbrace{\mathbf{H}_{i-1}^H \mathbf{E}_i}_{\rightarrow 0} \end{aligned}$$

where the cancellation of the product $\mathbf{H}_{i-1}^H \mathbf{E}_i$ is due to the principle of orthogonality (i.e., the error terms are orthogonal to the observed data). Denoting the cross correlation matrix

as $\mathbf{R}_i = \mathbb{E} [\mathbf{H}_{t-i}^H \mathbf{H}_t]$, we solve for the MMSE estimator,

$$\mathbf{W} = \mathbf{R}_0^{-1} \mathbf{R}_1.$$

In practice, the population correlation matrices are estimated via finite samples of size N ,

$$\hat{\mathbf{R}}_k = \frac{1}{N} \sum_j^N \mathbf{H}_{i-k}^H(j) \mathbf{H}_i(j),$$

where $\mathbf{H}_i(j)$ is the j -th sample in the training set. The MMSE estimator based on the sample correlation matrices is written as

$$\hat{\mathbf{W}} = \hat{\mathbf{R}}_0^{-1} \hat{\mathbf{R}}_1.$$

We can further simplify this estimator to a scalar, $\gamma \in \mathbb{R}$, as

$$\hat{\gamma} = \frac{\text{Trace}(\hat{\mathbf{R}}_1(k, l))}{\sum_k^{R_d} \sum_l^{N_b} \hat{\mathbf{R}}_0(k, l)},$$

where k (l) are the row (column) indices of the correlation matrices. The estimator in this case is

$$\hat{\mathbf{H}}_i = \hat{\gamma} \hat{\mathbf{H}}_{i-1}. \quad (3.3)$$

Under the estimator γ , we proposed to encode the error, \mathbf{E}_t , using a convolutional autoencoder, $f(\mathbf{E}_t)$,

$$\hat{\mathbf{E}}_i = g(f(\mathbf{E}_i, \vec{\theta}_e), \vec{\theta}_d),$$

where $\mathbf{E}_i = \mathbf{H}_i - \gamma \hat{\mathbf{H}}_{i-1}$. The base station has access to the estimators γ and $\hat{\mathbf{H}}_{i-1}$, and the resulting CSI estimate at t_i is

$$\hat{\mathbf{H}}_i = \gamma \hat{\mathbf{H}}_{i-1} + \hat{\mathbf{E}}_i \quad (3.4)$$

3.2.1 MarkovNet

In [58], we proposed MarkovNet, a deep differential autoencoder. Each timeslot of MarkovNet uses an instance of CsiNet-Pro with unique parameters. The network at the first timeslot (t_1) is trained directly on the CSI (\mathbf{H}_1). For all subsequent timeslots, t_i for $i \geq 2$, we use the MMSE estimator (3.3) to produce an error term \mathbf{E}_t , and the autoencoder in each timeslot is trained to produce an error estimate, $\hat{\mathbf{E}}_t$. The estimated error is added back per (3.4) to produce a refined estimate.

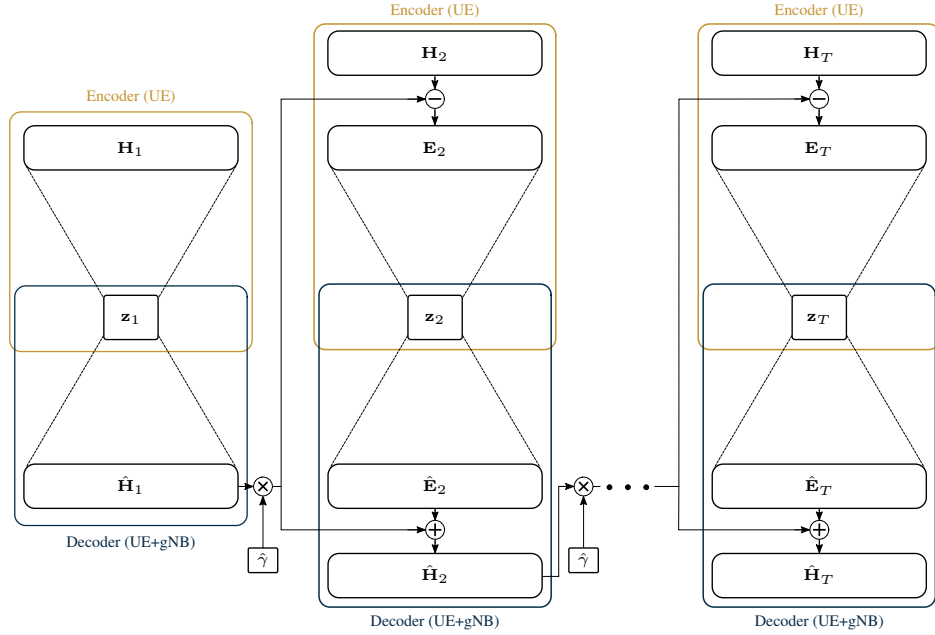


Figure 3.3: Abstract architecture for MarkovNet. Networks at t_i for $i \geq 2$ are trained to predict the estimation error, \mathbf{E}_i .

The resulting network requires no recurrent layers, resulting in a substantial reduction in computational complexity. Table 3.1 shows the number of parameters and FLOPs per timeslot for CsiNet-LSTM, MarkovNet, and CsiNet. The parameter count of MarkovNet

is on par with CsiNet, and CsiNet-LSTM requires orders of magnitude more parameters. While the number of FLOPs for MarkovNet is nearly 10 times smaller than CsiNet-LSTM, MarkovNet requires 5 to 10 times more FLOPs than CsiNet due to the increased kernel size of CsiNet-Pro.

Table 3.1: Model size/computational complexity of tested temporal networks (CsiNet-LSTM, MarkovNet) and comparable non-temporal network (CsiNet). M: million.

	Parameters			FLOPs		
	CsiNet-LSTM	MarkovNet	CsiNet	CsiNet-LSTM	MarkovNet	CsiNet
CR=1/4	132.7 M	2.1 M	2.1 M	412.9 M	44.5 M	7.8 M
CR=1/8	123.2 M	1.1 M	1.1 M	410.8 M	42.4 M	5.7 M
CR=1/16	118.5 M	0.5 M	0.5 M	409.8 M	41.3 M	4.7 M
CR=1/32	116.1 M	0.3 M	0.3 M	409.2 M	40.8 M	4.1 M
CR=1/64	115.0 M	0.1 M	0.1 M	409.0 M	40.5 M	3.9 M

3.2.2 Results

We compare MarkovNet with CsiNet-LSTM [52] on the indoor and outdoor COST2100 datasets (for details, see Section 1.3). For MarkovNet, we train the network at the first timeslot for 1000 epochs. In each subsequent timeslot, we initialize the network using the weights from the previous timeslot and train for 200 epochs. We use a batch size of 200. We perform a training/testing split of 75k/25k samples, and we estimate γ using the training set. To compare the estimation accuracy of each network, we report the NMSE.

Figure 3.4 shows the NMSE of MarkovNet and CsiNet-LSTM for four different compression ratios. For the indoor network, all instances of MarkovNet achieve lower NMSE than all instances of CsiNet-LSTM. In the outdoor scenario, each CR for MarkovNet demonstrates lower NMSE than the corresponding CR for CsiNet-LSTM. Between both channel scenarios, MarkovNet shows gradual improvement for subsequent timeslots if the CR is high enough while CsiNet-LSTM only improves gradually in the outdoor environment for $\text{CR} = \frac{1}{4}$. Figure 3.5 shows a random sample from the test set, \mathbf{H} , and the estimates produced by CsiNet-LSTM and MarkovNet for a CR of $\frac{1}{4}$. This sample contains three “peak” magni-

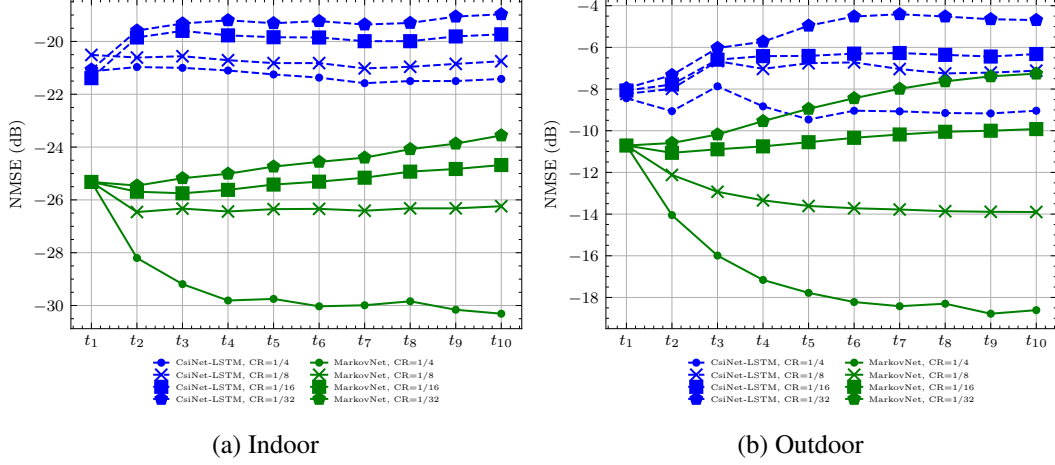


Figure 3.4: NMSE comparison of MarkovNet and CsiNet-LSTM at various compression ratios (CR).

tude regions. While both networks manage to capture the two larger samples, MarkovNet is able to recover the small peak magnitude region (green arrow) which CsiNet-LSTM fails to produce (red arrow).

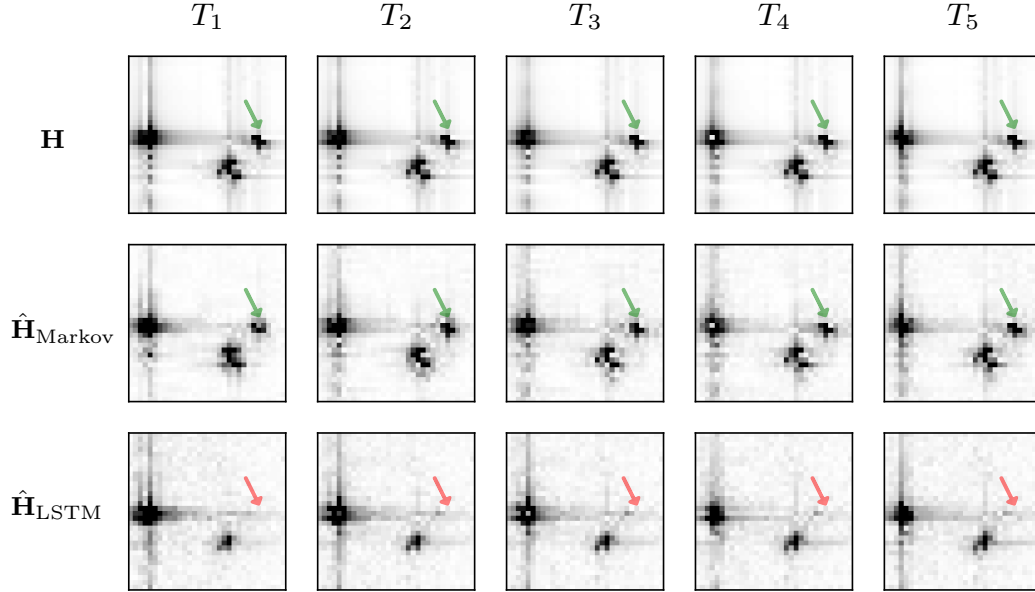


Figure 3.5: CSI (\mathbf{H}), MarkovNet estimates ($\hat{\mathbf{H}}_{\text{Markov}}$), and CsiNet-LSTM estimates ($\hat{\mathbf{H}}_{\text{LSTM}}$) across five timeslots (T_1 through T_5) on one outdoor channel sample from the test set, using $\text{CR} = \frac{1}{4}$.

To understand the effect of quantization on the network performance, we choose to use μ -law companding and uniform quantization on the latent feedback elements. We begin by

performing a logarithmic scaling on the feedback elements, x ,

$$f(x) = \frac{\text{sign}(x) \ln(1 + \mu|x|)}{\ln(1 + \mu)}, \quad 0 \leq |x| \leq 1. \quad (3.5)$$

After applying (3.5) to the signal, uniform quantization is applied to yield

$$\hat{x} = \Delta \left\lfloor \frac{f(x)}{\Delta} \right\rfloor \quad (3.6)$$

where $\Delta = 2^{-(b-1)}$ for b -bit quantization. Finally, an inverse logarithmic scaling is applied to quantized signal,

$$F(\hat{x}) = \frac{\text{sign}(\hat{x}) (1 + \mu)^{|\hat{x}|} - 1}{\mu}, \quad -1 \leq \hat{x} \leq 1. \quad (3.7)$$

In short, the described μ -law quantization scheme involves applying (3.5), then (3.6), then (3.7) to each feedback element. Figures 3.6 and 3.7 show the performance of MarkovNet and CsiNet-LSTM under μ -law quantization where $\mu = 255$.

In the Outdoor scenario, the performance of each network at each compression ratio does not change substantially for different numbers of quantization bits. In contrast, the performance for each network/compression ratio in the Indoor scenario drops appreciably for smaller quantization bits. We note that the performance of either network could potentially benefit from quantization during training, as all the results in Figures 3.4a and 3.4b are trained with continuous feedback.

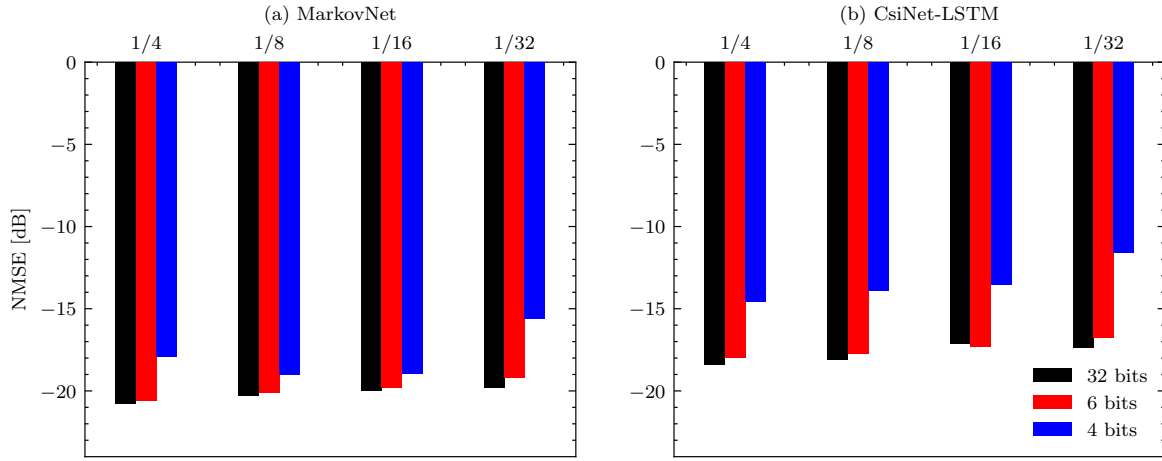


Figure 3.6: NMSE comparison of MarkovNet and CsiNet-LSTM for the Indoor scenario with feed-back subject to μ -law quantization using fixed step size, $\Delta = 2^{-(b-1)}$, for b bits.

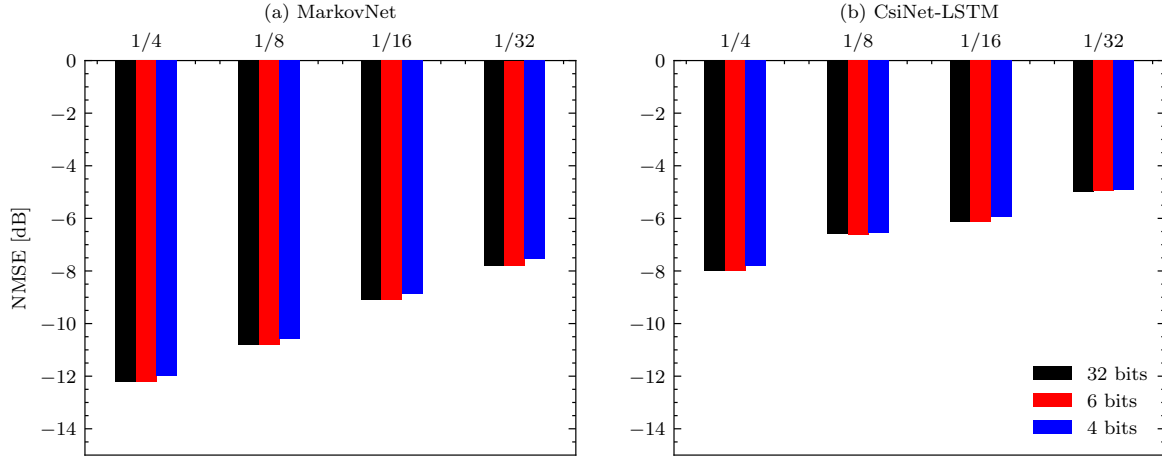


Figure 3.7: NMSE comparison of MarkovNet and CsiNet-LSTM for the Outdoor scenario with feed-back subject to μ -law quantization using fixed step size, $\Delta = 2^{-(b-1)}$, for b bits.

Chapter 4

Spectrum-efficient Pilot-based CSI

Feedback

This chapter details an estimator for the UE-side angular-delay domain CSI based on a limited number of spatial-frequency domain pilots. This scheme adheres to the 3GPP standards for pilot allocation across time-frequency resources as described in Section 1.2.

Section 4.1 details our proposed pilots-to-delay estimator (P2DE), and Figure 4.1 demonstrates the operating principle behind P2DE. Section 4.1.1 describes off-diagonal regularization as a countermeasure for ill-conditioned CSI matrices. Section 4.1.2 explicitly links the proposed P2DE to the 3GPP placement of CSI-RS/DMRS resource elements and describes our proposed diagonal pilot pattern which adheres to LTE/NR specifications. Section 4.2 describes an extension of our previously proposed differential encoding network which uses heterogeneous CNNs for different timeslots. Finally, Section 4.3 presents results for the P2DE and our proposed heterogeneous differential encoding networks.

4.1 Pilots-to-delay Estimator (P2DE)

Denote $\boldsymbol{\eta}_i \in \mathbb{C}^{N_f}$ as the i -th row of the spatial-frequency matrix \mathbf{H} , and denote the downsampled version of $\boldsymbol{\eta}_i$ as $\boldsymbol{\eta}_{d,i} \in \mathbb{C}^{M_f}$ where $M_f \ll N_f$. Thus, the spatial-frequency

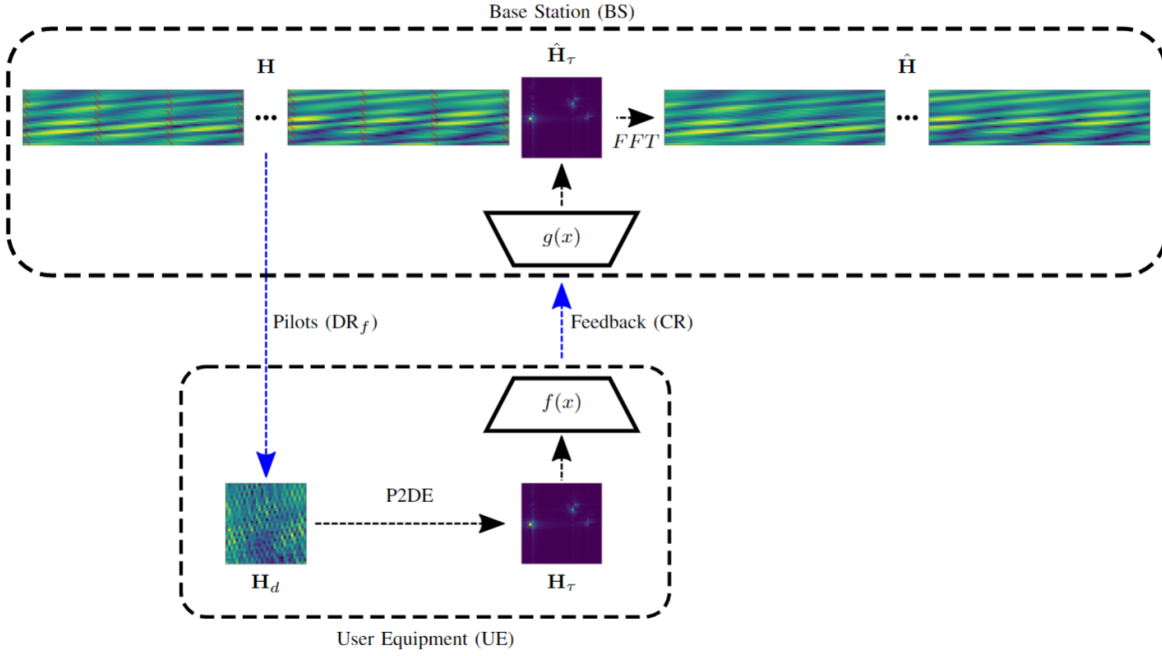


Figure 4.1: Compressive CSI estimation based on linear P2D estimator. First, we use downlink pilots to generate a sparse, frequency domain CSI estimate of size $M_f \ll N_f$. We then apply the P2D estimator, $\mathbf{Q}_{N_t}^\dagger$ of (4.5), to establish the truncated delay domain CSI estimate. We train a learnable encoder, $f(x)$, and decoder, $g(x)$, to compress and decode the feedback, respectively. The gNB recovers the frequency domain CSI from the decoded delay domain CSI estimate.

CSI, \mathbf{H} , and its downsampled counterpart, \mathbf{H}_d , can be written as,

$$\mathbf{H} = \begin{bmatrix} \boldsymbol{\eta}_1 \\ \boldsymbol{\eta}_2 \\ \vdots \\ \boldsymbol{\eta}_{N_b} \end{bmatrix} \in \mathbb{C}^{N_b \times N_f}, \quad \mathbf{H}_d = \begin{bmatrix} \boldsymbol{\eta}_{d,1} \\ \boldsymbol{\eta}_{d,2} \\ \vdots \\ \boldsymbol{\eta}_{d,N_b} \end{bmatrix} \in \mathbb{C}^{N_b \times M_f}. \quad (4.1)$$

$\boldsymbol{\eta}_{d,i}$ is related to $\boldsymbol{\eta}_i$ by the downsampling matrix for the i -th antenna port, \mathbf{P}_i , as

$$\boldsymbol{\eta}_{d,i} = \boldsymbol{\eta}_i \mathbf{P}_i \quad \forall i \in [1, \dots, N_b]. \quad (4.2)$$

Denote the delay-domain CSI vector, $\tilde{\boldsymbol{\eta}}_i$, which is defined as

$$\tilde{\boldsymbol{\eta}}_i \mathbf{F} = \boldsymbol{\eta}_i, \quad (4.3)$$

where \mathbf{F} is the $\mathbb{C}^{N_f \times N_f}$ discrete Fourier transform (DFT) matrix. To relate the frequency domain pilots to the delay domain, we apply the pilot downsampling matrix \mathbf{P}_i to both sides of 4.3,

$$\begin{aligned} \tilde{\boldsymbol{\eta}}_i \mathbf{F} \mathbf{P}_i &= \boldsymbol{\eta}_i \mathbf{P}_i \\ \tilde{\boldsymbol{\eta}}_i \mathbf{Q}_i &= \boldsymbol{\eta}_{d,i} \end{aligned} \quad (4.4)$$

where $\mathbf{Q}_i = \mathbf{F} \mathbf{P}_i \in \mathbb{C}^{N_f \times M_f}$ is the downsampled DFT matrix. Leveraging the sparsity of CSI data in the delay domain (see Section 2.1.1, Figure 2.1), many works choose to feedback and compress the truncated delay domain vectors, $\tilde{\boldsymbol{\eta}}_{c,i} \in \mathbb{C}^{N_t}$. The zero-padded vector $\tilde{\boldsymbol{\eta}}_i$ defined as

$$\tilde{\boldsymbol{\eta}}_i = [\tilde{\boldsymbol{\eta}}_{c,i}, \mathbf{0}_{N_f - N_t}]. \quad (4.5)$$

Based on 4.4, the delay domain can be related directly to the pilots by taking the pseudoinverse,

$$\begin{aligned}\tilde{\boldsymbol{\eta}}_i \mathbf{Q}_i \mathbf{Q}_i^T &= \boldsymbol{\eta}_{d,i} \mathbf{Q}_i^T \\ \tilde{\boldsymbol{\eta}}_i &= \boldsymbol{\eta}_{d,i} \mathbf{Q}_i^T (\mathbf{Q}_i \mathbf{Q}_i^T)^{-1} \\ &= \boldsymbol{\eta}_{d,i} \mathbf{Q}_i^\# \end{aligned} \tag{4.6}$$

4.1.1 Regularization of P2DE

When the pilot patterns \mathbf{P}_i are equidistant and regularly spaced, the P2DE matrices $\mathbf{Q}_i \mathbf{Q}_i^T$ are typically well-conditioned. However, more irregular patterns can result in ill-conditioned matrices $\mathbf{Q}_i \mathbf{Q}_i^T$, making these matrix inversion unstable.

To compensate for this ill-conditioning, we propose to use off-diagonal regularization (ODIR) to condition the P2DE matrices. Denote $\mathbf{R} = \mathbf{Q}_i \mathbf{Q}_i^T$ and R_{ij} as the element in the i -th row and j -th column of the matrix. We select a non-negative real scaling factor $\delta \in \mathbb{R}^+$ to scale down the off-diagonal elements of \mathbf{R} . The element of the resulting ODIR matrix, \mathbf{R}_{ODIR} , are written as

$$R_{ij,\text{ODIR}} = \begin{cases} R_{ij} & \text{if } i = j \\ \frac{R_{ij}}{1+\delta} & \text{if } i \neq j. \end{cases} \tag{4.7}$$

4.1.2 Diagonal Pilot Allocations for 3GPP Standards

As discussed in Section 1.2, 3GPP specifications describe the allocation of pilots to time-frequency resources in 4G/LTE [10, 59] and 5G/NR [11] radio networks, where the reserved resource elements are called CSI reference signals (CSI-RS) for the former and demodulation reference signals (DMRS) for the latter.

In order to connect the P2DE as described in Section 4.1 to the 3GPP specifications, we

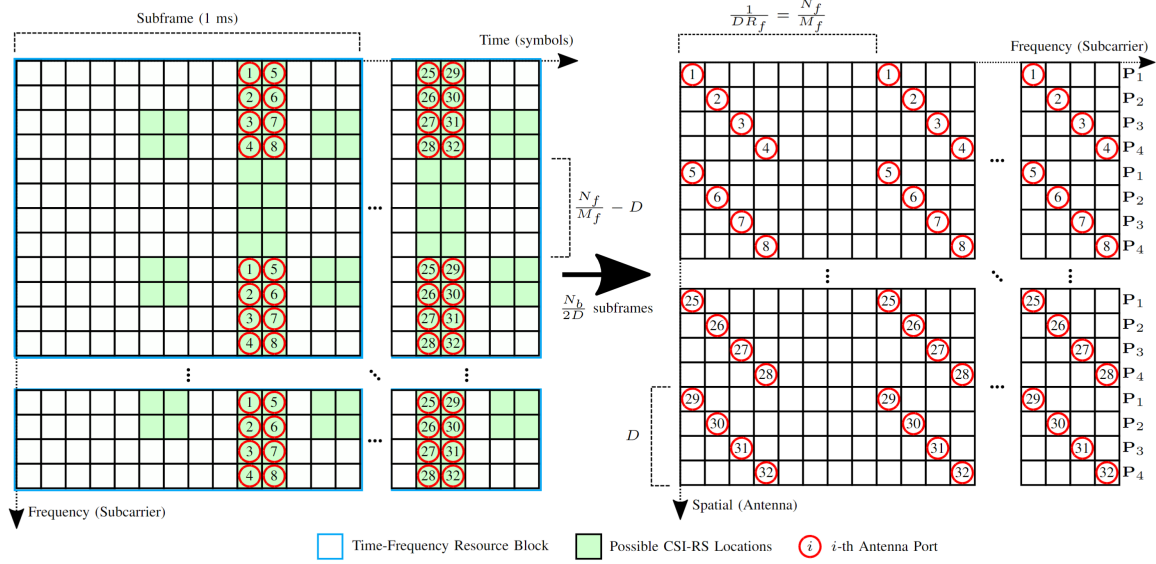


Figure 4.2: (a) LTE Resource Blocks and CSI-RS locations where antenna port pilots are allocated. (b) Schematic for diagonal pilots with relevant parameters, size of diagonal D and frequency down-sampling ratio DR_f . In this diagram, $N_b = 32$, $D = 4$, $DR_f = \frac{1}{8}$. The pilot matrix P_j indicates the downsampling pattern for the j -th element of the diagonal pattern. The number of subframes necessary to populate (b) is inversely proportional to D .

must specify the corresponding pilot patterns in the time-frequency grid. In Figure 4.2, we show an example of our proposed ‘diagonal’ pilot pattern in an LTE network using CSI-RS locations. We refer to this pattern as diagonal since it is diagonal in the spatial-frequency domain. The benefit of the diagonal pattern can be understood by considering the time needed to acquire downsampled CSI matrix, \mathbf{H}_d .

Algorithm 4.1 shows the process for acquiring the delay domain P2DE from sparse frequency domain pilots.

4.2 Heterogeneous Differential Encoding with P2DE

Chapter 3 introduced the concept of differential encoding for CSI feedback compression. The delay domain P2DE CSI introduced in this Chapter can also be used in the differential encoding framework. Figure 4.5 showcases the data path when utilizing the P2D estimates with a differential encoding network.

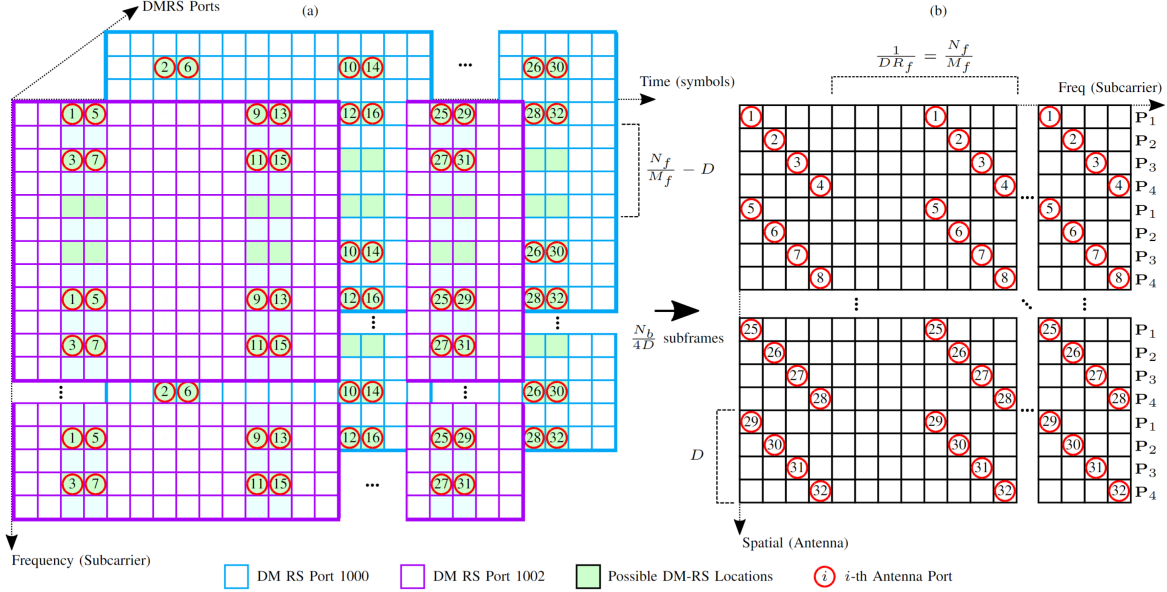


Figure 4.3: (a) 5G NR Resource Blocks and DMRS locations where antenna port pilots are allocated. (b) Schematic for diagonal pilots with relevant parameters, size of diagonal D and frequency down-sampling ratio DR_f . In this diagram, $N_b = 32, D = 4, DR_f = \frac{1}{8}$. The pilot matrix P_j indicates the downsampling pattern for the j -th element of the diagonal pattern. The number of subframes necessary to populate (b) is inversely proportional to D .

Algorithm 4.1 Pilots-to-delay Estimator (P2D) for Diagonal Pilot Pattern

- 1: **Input:** P2DE Matrices, $\mathbf{Q}_{c,j}^\#, j \in \{1, \dots, D\}$
 - 2: **Input:** Pilot spatial-frequency CSI, $\mathbf{H}_d \in \mathbb{C}^{N_b \times M_f}$
 - 3: **Initialize:** Spatial-delay CSI, $\tilde{\mathbf{H}}_\tau \in \mathbb{C}^{N_b \times N_t}$
 - 4: **Initialize:** Angular-delay CSI estimate, $\mathbf{H}_\tau \in \mathbb{C}^{N_b \times N_t}$
 - 5: **for** $i = 1, 2, \dots, N_b$ **do**
 - 6: **# Index for j -th pilot matrix**
 - 7: $j = ((i - 1) \bmod D) + 1$
 - 8: **# Apply P2D to i -th antenna port**
 - 9: $\boldsymbol{\eta}_{d,i} = \mathbf{H}_d(i, :)$
 - 10: $\tilde{\mathbf{H}}_\tau(i, :) = \boldsymbol{\eta}_{d,i} \mathbf{Q}_{c,j}^\#$
 - 11: **end for**
 - 12: **# Convert from spatial to angular**
 - 13: $\mathbf{H}_\tau = \mathbf{F}_{N_b} \tilde{\mathbf{H}}_\tau$
 - 14: **Return** \mathbf{H}_τ
-

The prior work proposed a differential encoding network that used an identical autoencoder at each timeslot. We refer to such a network as ‘homogeneous.’ In contrast, we can consider a ‘heterogeneous’ network, where we use different network architectures at different timeslots.

In this section, we describe a heterogeneous differential encoder which combines deep compressed sensing with deep autoencoders.

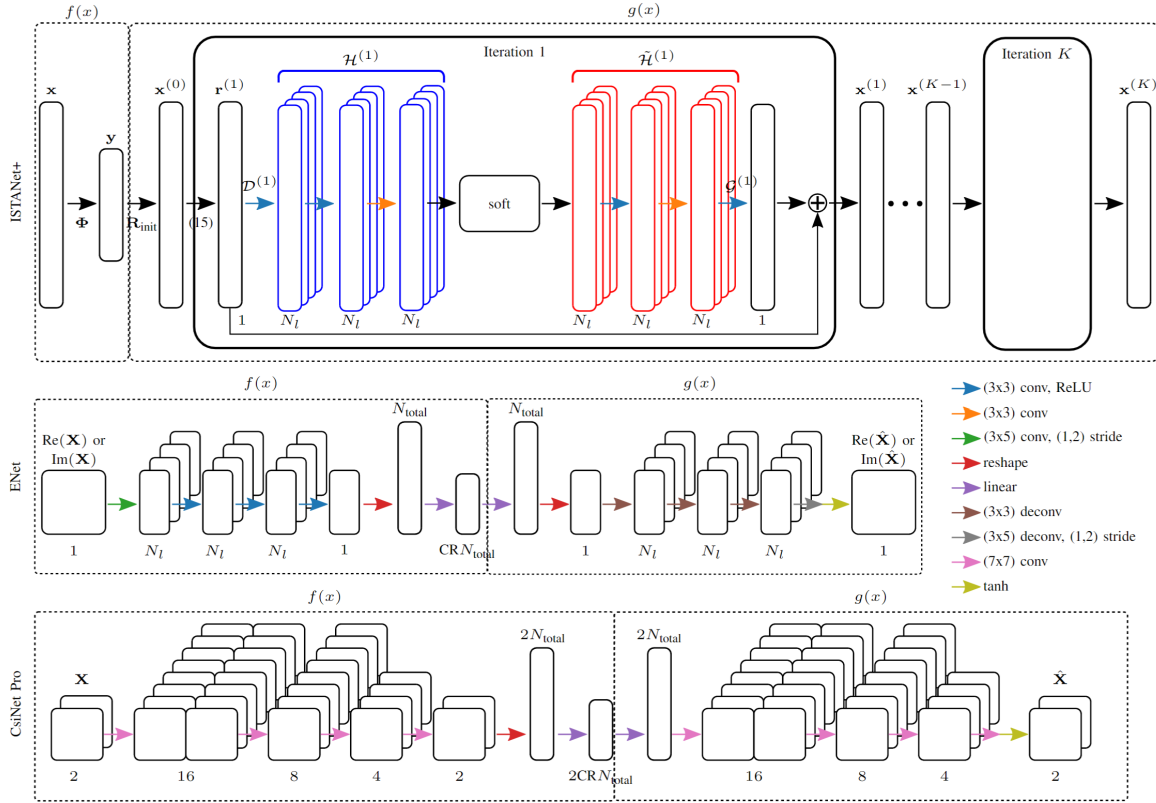


Figure 4.4: Compressive CSI estimation architectures used in this work. $f(x)$ denotes the encoder, and $g(x)$ denotes the decoder. $N_{\text{total}} = N_b N_t$ is the size of the real or imaginary channel. N_l is the number of latent channels in a convolutional layer.

4.2.1 Iterative Optimization Networks for Compressed Sensing-based CSI Feedback

While CNN autoencoders have been dominant in CSI estimation, recent work from image processing has shown promise in using trainable CS algorithms based on CNNs. These

works treat iterative CS algorithms as sequential networks by “unrolling” them into discrete blocks [60, 61]. Investigating unrolled CS algorithms for CSI estimation warrants consideration, as CS algorithms can have guaranteed convergence under mild sparsity conditions (in contrast with CNNs autoencoder approaches, which do not have such guarantees). Since CSI data exhibits sparsity in the delay domain, specifying an appropriate compressed sensing approach could provide appreciable performance gains in our differential CSI encoding architecture.

To exploit the temporal coherence of the MIMO channel, we propose to construct a differential encoding network using an unrolled optimization network based on a trainable version of the iterative shrinkage-thresholding algorithm (ISTA), called ISTANet+ [61]. See the top of Figure 4.4 for a diagram of ISTANet+. Denote measurement matrix for the ISTANet+ as

$$\Phi \in \mathbf{R}^{N_{\text{total}} \text{CR} \times N_{\text{total}}}. \quad (4.8)$$

For compressed sensing approaches, the measurement matrix is analogous to the ‘encoder’ for autoencoder approaches, i.e., $f(x) = \Phi x$. The ‘decoder’ consists of K iterations of the following update steps,

$$\mathbf{r}^{(k)} = \mathbf{x}^{(k-1)} - \rho^{(k)} \Phi^\top (\Phi \mathbf{x}^{(k-1)} - \mathbf{y}) \quad (4.9)$$

$$\mathbf{x}^{(k)} = \mathbf{r}^{(k)} + \mathcal{G}^{(k)} \left(\tilde{\mathcal{H}}^{(k)} \left(\text{soft} \left(\mathcal{H}^{(k)}(\mathcal{D}^{(k)}(\mathbf{r}^{(k)}), \theta^{(k)}) \right) \right) \right) \quad (4.10)$$

where $\mathbf{y} = \Phi \mathbf{x}$, $\mathbf{x}^{(0)} = \mathbf{R}_{\text{init}} \mathbf{y}$, and $\mathbf{R}_{\text{init}} = \mathbf{X} \mathbf{Y} (\mathbf{Y} \mathbf{Y}^\top)^{-1}$ is the initialization matrix for the training data matrix $\mathbf{X} = [\mathbf{x}_1, \mathbf{x}_2, \dots, \mathbf{x}_{N_{\text{train}}}]$ and the training measurement matrix $\mathbf{Y} = [\mathbf{y}_1, \mathbf{y}_2, \dots, \mathbf{y}_{N_{\text{train}}}]$. ‘soft(\cdot)’ denotes the soft threshold function,

$$\text{soft}(x, \theta) = \text{sign}(x) \text{ReLU}(|x| - \theta). \quad (4.11)$$

$\mathcal{G}^{(k)}, \mathcal{D}^{(k)}, \mathcal{H}^{(k)}, \tilde{\mathcal{H}}^{(k)}$ indicate trainable nonlinear mappings (in this case, CNNs), and $\mathcal{H}^{(k)}, \tilde{\mathcal{H}}^{(k)}$ are subject to the symmetry constraint $\mathcal{H}^{(k)} \circ \tilde{\mathcal{H}}^{(k)} = \mathbf{I}$.

In the proposed differential encoding scheme, we use an instance of ISTANet+ in the first timeslot, t_1 , with a large compression ratio such that $\text{CR}_{t_1} \geq \text{CR}_{t_i}$ for all $i > 1$. This choice in compression ratio allows us to initialize the network with a high-quality estimate at the first timeslot. Notably, the training data matrix, \mathbf{X} , differs between timeslots. For the first timeslot, the data vectors \mathbf{x}_i are vectorized versions of the CSI matrices,

$$\mathbf{x}_j = \text{vec} \left(\mathbf{H}_{\tau,1}^{(j)} \right) \text{ for } j \in [N_{\text{train}}]. \quad (4.12)$$

However, the data vectors for all other timeslots are vectorized versions of the error matrices,

$$\mathbf{x}_j = \text{vec} \left(\bar{\mathbf{E}}_i^{(j)} \right) \text{ for } j \in [N_{\text{train}}]. \quad (4.13)$$

Denote the parameters for ISTANet+ in the t_i -th timeslot as $\Theta_{t_i} = \{\mathcal{G}^{(k)}, \mathcal{D}^{(k)}, \mathcal{H}^{(k)}, \tilde{\mathcal{H}}^{(k)}, \theta^{(k)}, \rho^{(k)}\}_{k=1}^K$.

The loss function is a weighted sum of the MSE and the symmetry constraint, i.e.,

$$L(\Theta_{t_i}) = L_{\text{MSE}} + \alpha L_{\text{sym}} \quad (4.14)$$

$$L_{\text{MSE}} = \frac{1}{N_{\text{batch}} N_{\text{total}}} \sum_{i=1}^{N_{\text{batch}}} \|\mathbf{x}_i^{(K)} - \mathbf{x}_i\|_2^2 \quad (4.15)$$

$$L_{\text{sym}} = \frac{1}{N_{\text{batch}} N_{\text{total}}} \sum_{i=1}^{N_{\text{batch}}} \sum_{k=1}^K \|\tilde{\mathcal{H}}^{(k)}(\mathcal{H}^{(k)}(\mathbf{x}_i)) - \mathbf{x}_i\|_2^2 \quad (4.16)$$

where $N_{\text{total}} = N_b N_t$ is the size of the truncated CSI matrix, K is the number of iterations in ISTANet+, and N_{batch} is the batch size used during training. As denoted in equations (4.12) and (4.13), the vectors \mathbf{x}_i depend on the timeslot.

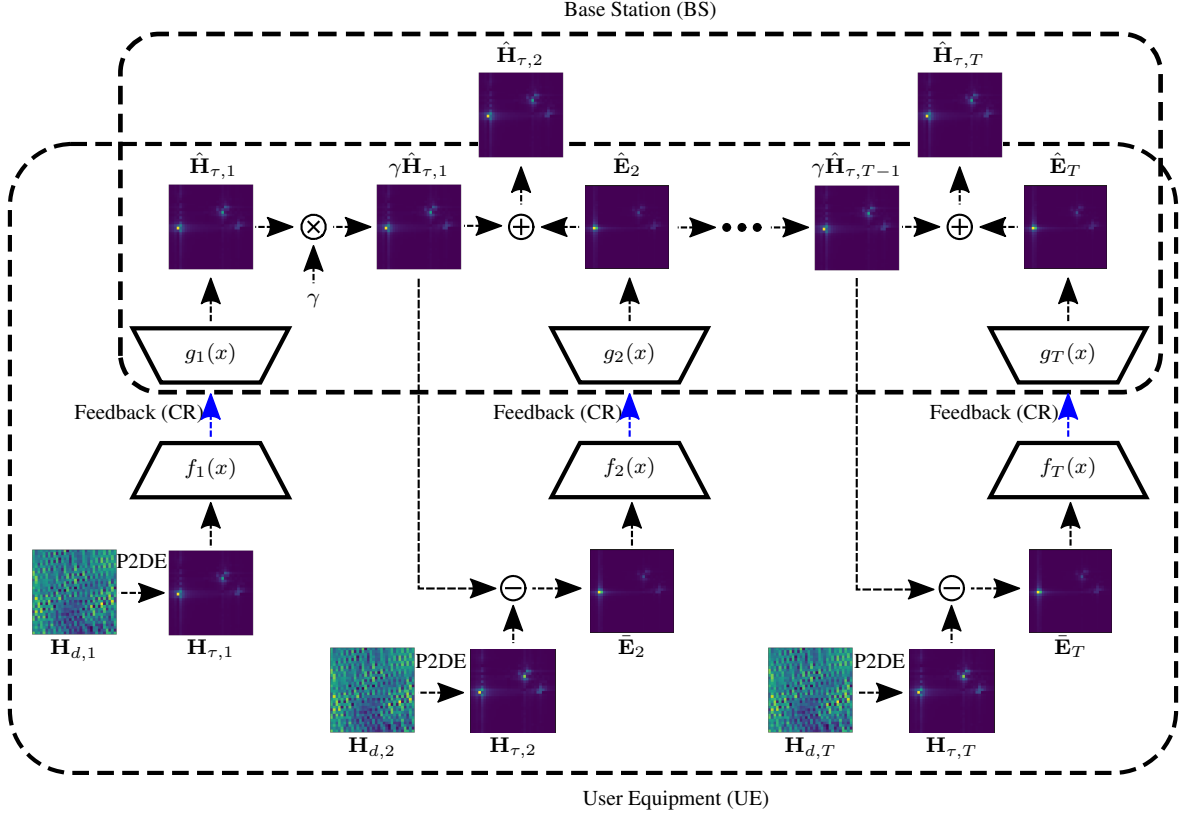


Figure 4.5: Diagram of a CSI estimation network using compressed differential feedback based on the linear P2DE. First, downlink pilots are used to estimate a downsampled frequency domain CSI estimate, $\tilde{\mathbf{H}}_t \in \mathbb{C}^{N_b \times M_f}$ where $M_f \ll N_f$ at the t -th timeslot. Then, the P2DE $\mathbf{Q}_{N_t}^\#$ of Algorithm 4.1 is applied to estimate $\tilde{\mathbf{H}}_t$. After P2DE, the learnable transforms $f_t(x)$ and $g_t(x)$ are used to compress and decode the feedback, respectively. For $t = 1$, the encoder/decoder are applied directly to $\tilde{\mathbf{H}}_1$. In all subsequent timeslots ($t > 1$), the differential term \mathbf{E}_t is compressed and fed back.

4.3 Results

4.3.1 Accuracy of P2DE

We assess the accuracy of the P2DE under values of M_f and D . Fig. 4.6 demonstrates the accuracy of the P2DE at the UE (i.e., before compression and feedback) for different frequency downsampling ratios. The P2DE achieves impressive accuracy even under aggressive values of DR_f (e.g., better than -30dB at $\text{DR}_f = \frac{1}{8}$). Additionally, the effect of increasing the diagonal size, D , is apparent at larger compression ratios (i.e., $\text{CR} \geq \frac{1}{8}$), where the accuracy of the P2DE to a value as low as -25dB . For smaller compression ratios (i.e., $\text{CR} \leq \frac{1}{16}$), increasing D has a marginal effect on the accuracy of the P2DE.

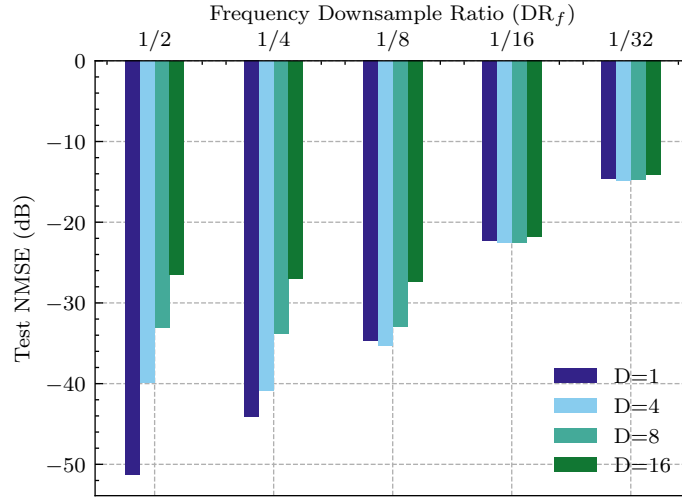


Figure 4.6: P2D estimation performance under different frequency downsampling ratios ($\text{DR}_f = \frac{M_f}{N_f}$) and diagonal dimensions (D) for the Outdoor COST2100 dataset. Downsampling is done along the frequency axis.

We assess the accuracy of the P2DE assuming noise from pilot estimation. To simulate pilot estimation error, we use additive Gaussian noise,

$$\hat{\mathbf{H}}_d = \mathbf{H}_d + \mathbf{N}_d$$

where the elements of \mathbf{N}_d , $\mathbf{N}_d(i, j) \sim \mathcal{N}(0, \sigma^2)$ for $i \in [1, 2, \dots, N_b], j \in [1, 2, \dots, M_f]$.

To achieve different SNR values for $\hat{\mathbf{H}}_d$, we simply vary the noise variance σ^2 , and we use the P2DE at different pilot estimation noise levels. Figure 4.7 shows the accuracy of the P2DE for different values of σ^2 .

In addition to varying the pilots estimation SNR, we also showcase the effect of varying δ (i.e., the ODIR parameter as described in Section ??). We observe that δ helps the P2DE achieve better performance under both low-noise and noisy conditions, i.e.,

- **Low-noise condition (SNR = −20 dB):** The P2DE goes from −8 dB to −22 dB for $\delta = 0$ and $\delta = 0.5$, respectively.
- **Noisy condition (SNR ≥ −10 dB):** The P2DE goes from −9 dB to −30 dB for $\delta = 0$ and $\delta = 0.5$, respectively.

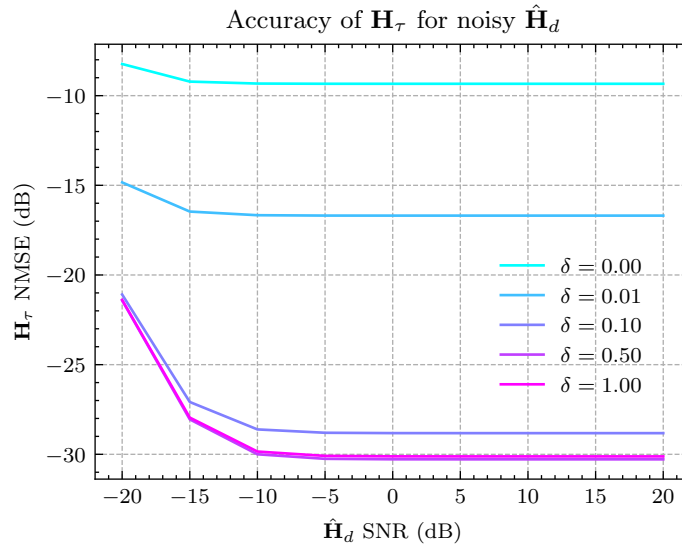


Figure 4.7: Accuracy of P2DE output, \mathbf{H}_τ , assuming noisy pilots, $\hat{\mathbf{H}}_d$. Additive Gaussian noise is used to model the error inherent in pilot estimation. Here, $D = 4$, $\text{DR}_f = \frac{1}{32}$.

4.3.2 P2DE Compression Network Comparison

Having assessed the initial accuracy of the P2DE at the UE, we now apply a deep learning network to compress the output of the P2DE. Figure 4.8 demonstrates the accuracy of IS-

TANet+ [61] for multiple compression ratios (CR) using the P2DE as its input. For progressively smaller compression ratios, the accuracy of ISTANet+ remains stable until $DR_f = \frac{1}{32}$, at which point the network’s performance degrades.

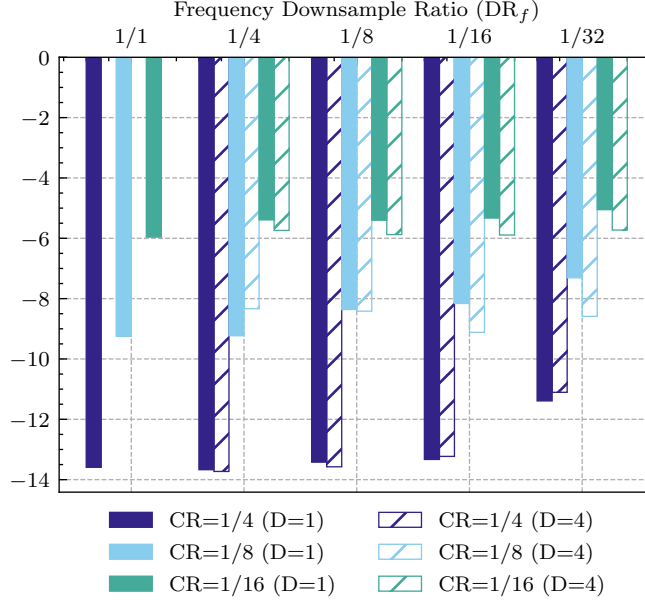


Figure 4.8: Performance of ISTANet+ for multiple compression ratios using P2D estimates with different downsampling ratios ($DR_f = \frac{M_f}{N_f}$) for the Outdoor COST2100 dataset. Non-diagonal pattern ($D = 1$) is compared with a diagonal pattern of size $D = 4$. Performance for $DR_f = 1/1$, $D = 4$ is omitted since it is equivalent to the $DR_f = 1$, $D = 1$ case.

In addition to ISTANet+, we assess the accuracy deep CNN autoencoders using P2DE as an input. Figure 4.9 shows the accuracy of ISTANet+ compared to ENet [62] and SphNet [43]. The performance of ISTANet+ is better than both ENet and SphNet at larger compression ratios ($CR \in [\frac{1}{4}, \frac{1}{8}]$), and the performance of ISTANet+ and ENet is comparable at $CR = \frac{1}{16}$.

To assess the accuracy of these networks under quantization, we also conduct an experiment where the latent feedback elements are subjected to μ -law companding and uniform quantization (as described in Section 3.2.2). We present these results in Figure 4.10.

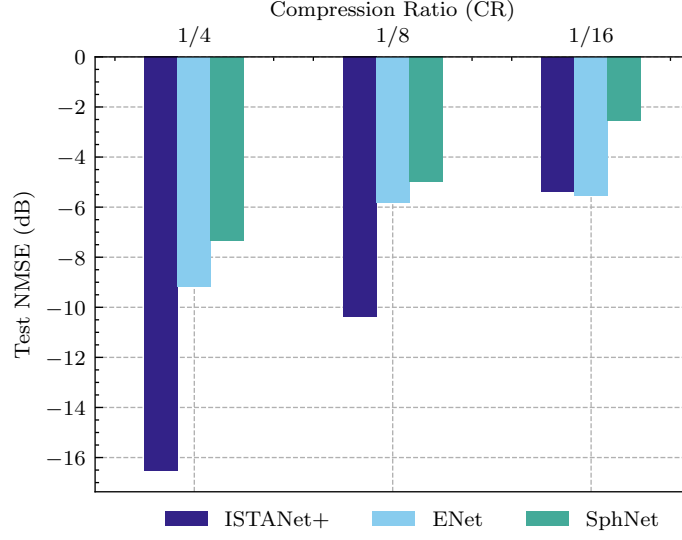


Figure 4.9: Performance comparison for different feedback compression networks using P2D estimates ($DF_f = 1/16, D = 4$) for Outdoor COST2100 dataset. For all tested networks, we use $N_{\text{phase}} = 4$, resulting in an augmented training set with 80k samples.

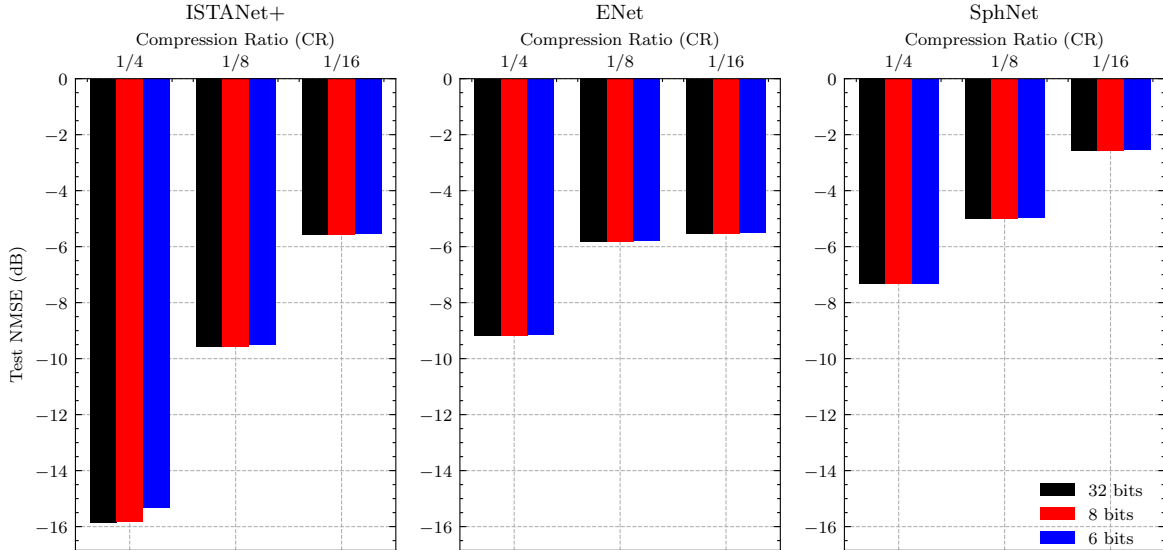


Figure 4.10: Tested networks where feedback is subject to μ -law companding ($\mu = 255$) and uniform quantization for different numbers of quantization bits. P2DE parameters are $D = 4, DR_f = \frac{1}{16}$.

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