

A 64 Channel 3T Array Coil for Highly Accelerated Fetal Imaging at 22 Weeks of Pregnancy

by

Mark H. Spatz

Submitted to the Department of Electrical Engineering and Computer
Science

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Abstract

MRI is an attractive tool for fetal imaging due to its unique ability to provide detailed anatomical and physiological data in an inherently safe manner. In practice, fetal MRI is limited by fetal motion, inherently poor SNR in the maternal abdomen, and widely varying body shapes. A 64 channel receive array designed to conform to a range of body shapes at 22 weeks of pregnancy was built and tested. Compared to standard product arrays, the coil provides 5SNR in the fetal brain region of an anthropomorphic phantom and allows increasing SENSE acceleration factor from R=4 to R=5.

Thesis Supervisor: Lawrence L. Wald
Title: Professor of Radiology, Harvard Medical School

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Chapter 1

Introduction

MRI is increasingly used in addition to ultrasound to evaluate potential fetal disorders in routine clinical practice. Indeed, MRI provides a higher soft tissue contrast than ultrasound in the fetus and reproductive organs. MRI also has the potential to provide valuable physiological information through spectroscopic and diffusion weighted imaging. In practice, the problem of unpredictable and nonrigid fetal motion limits fetal MRI to fast single shot T2 weighted sequences which have poor tissue contrast, low SNR, and cannot provide detailed physiological information.

High density arrays are needed to minimize acquisition times and maximize SNR. A standard fetal MRI protocol employs a spine array and a flexible body array to reach a total of approximately 34 channels. (HOW MANY WOULD BE OPTIMAL, CITE PRUSSMAN) This limits the acceleration factors that can be achieved. Additionally, these general purpose coils are often unable to completely conform to the varied anatomy of pregnant patients, leaving some receive elements distant to the abdomen. In this work, we designed, built, and tested a semi-adjustable anatomically shaped 64 channel array coil for fetal imaging at 22 weeks of pregnancy on a 3T MAGNETOM Skyra system (Siemens Healthcare GmbH, Erlangen, Germany) .

Chapter 2

Background

Magnetic resonance imaging is, as the name suggests, enabled by the phenomenon of magnetic resonance. Atoms with an odd number of protons or neutrons possess net nuclear spin, and therefore effectively have small magnetic moments which can be made to resonate at a precisely defined frequency in the presence of a static magnetic field. Hydrogen (${}^1\text{H}$) is such an atom, and is the main candidate for clinical imaging because of the abundance of H_2O in living things [2].

Chapter 3

Array Design

3.1 Physical Design

The 22 week fetal array is designed to provide good surface area coverage and close physical fit on a range of body types at 22 weeks of pregnancy. It consists of a rigid posterior panel that attaches directly to the patient table and a group of anterior and lateral panels that can be freely positioned on the patient. The two lateral panels are attached to the anterior panel with hinges to provide a degree of freedom. The patient facing surfaces of these panels are modeled after segmented images of a 22 weeks pregnant volunteer. The precise geometry of the hinged panel assembly was arrived at through iterative fit tests on pregnant volunteers.

The coil formers and housings were designed in Rhinoceros (Robert McNeel & Associates, WA, USA) and printed in poly carbonate on a Fortus 400mc 3D printer (Stratasys, Ltd., MN, USA).

3.2 Array Construction

The array consists of four distinct groups of coil elements. The posterior panel contains 24 loops, each with a diameter of approximately 9cm. The anterior panel contains 20 loops, with a median loop diameter of 8cm and with several outliers in the non-hexagonally tiled area. The two anterior panels contain 10 7cm loops each. The

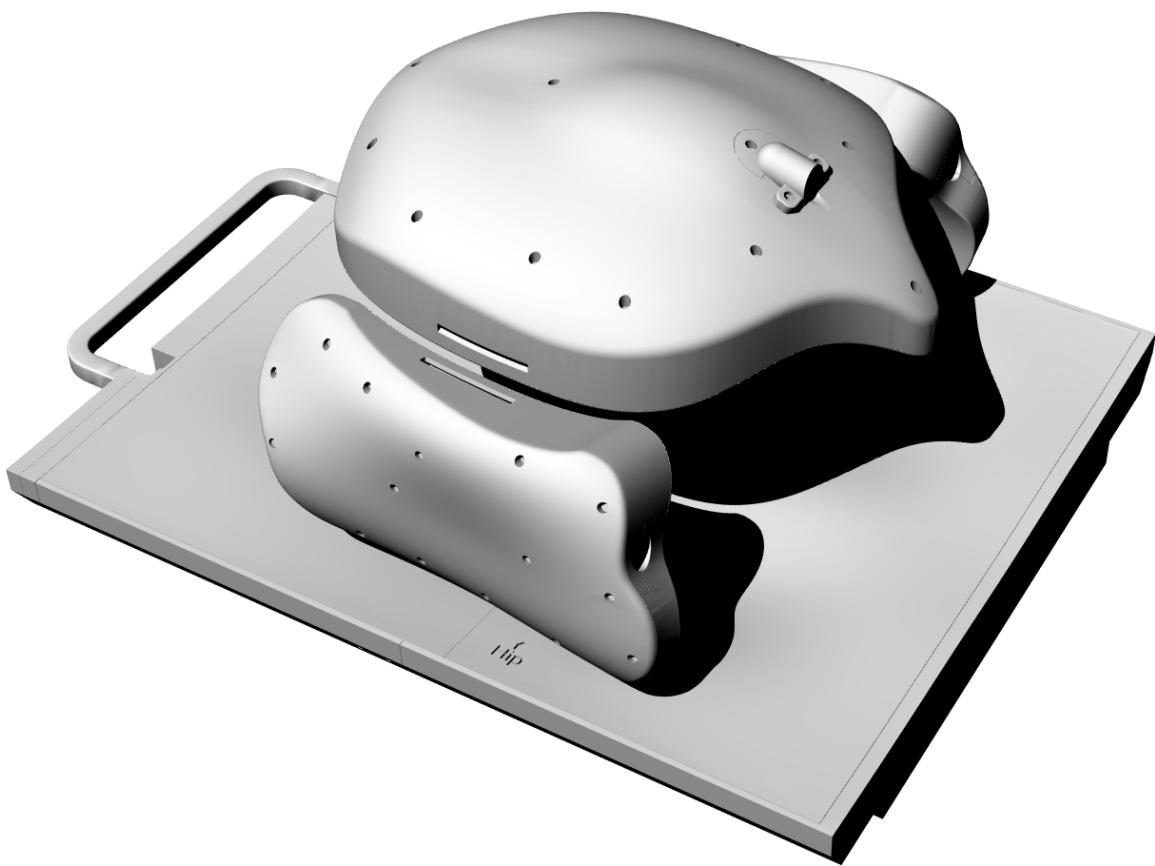


Figure 3-1: Computer rendering of array panels and housings.

loops in each panel are for the most part arranged in a hexagonal tiling pattern that allows each loop to be critically overlapped with all of its neighbors, thus minimizing inductive coupling between neighboring loops [?]. The loop layout is shown in detail in 7-13.

Individual loops were constructed from 16 gauge tin plated copper wire, with bridges bent into the wires to allow them to cross each other without touching. A schematic of the loop circuitry is shown in 4-1. Chapter 4 contains a detailed explanation of the function of the loop circuit.

The finished coil is shown in figure 3-2 posed on the pregnant abdomen phantom used extensively in testing. A view of the internal construction and wiring is shown in figure 3-3.

3.3 Cable Traps

Precautions must be taken to prevent large currents from developing on internal and external wiring during the RF transmit phase. Such uncontrolled currents could pose a fire/safety hazard, and at the very least would interfere with the sequence being run. Common mode chokes spaced every 20cm on all internal and external prevent the induced currents from growing too large. Due to the high magnetic field the array operates in, ferrite chokes are not an option. Instead, tuned resonant traps are constructed. Two types of traps were used in this array.

3.3.1 Helical Traps

The operation of the resonant helical traps visible in fig. 3-3 is easy to understand. The jacketed wire bundle is wound around a helical former, forming an air core inductor. High voltage capacitors are then connected across the turns of the inductor, forming a parallel LC tank. At resonance, the trap presents a high impedance to common mode currents flowing in the jacket. This kind of trap can hold off hundreds of volts, and has a high Q. It is used as the first cable trap inside each array panel, and inside the table plug.



Figure 3-2: Finished coil, posed on 22 week pregnant abdomen phantom.



Figure 3-3: View of internal array construction and wiring.

3.3.2 Bazooka Trap

The bazooka trap can be thought of as a physically short bazooka balun that has been electrically lengthened to $\frac{\lambda}{4}$ by shunting the open end with a capacitor. A cylindrical plastic spacer is printed in two halves. The outside surface of each half is covered in copper tape, with a gap left in the middle. The two halves are placed around the wire bundle and soldered together, and each end of the balun is soldered to the braided wire jacket. The gap in the copper tape is bridged with nonmagnetic capacitors selected such that the structure resonates at the desired frequency. An additional layer of copper shielding on the balun enclosure stabilizes the capacitance between the two ends of the balun so that external loading does not affect its resonant frequency. This kind of trap is more compact and consumes less wire length than the helical trap, but cannot hold off as much voltage and has a lower Q. It is placed periodically on long runs of external wiring.

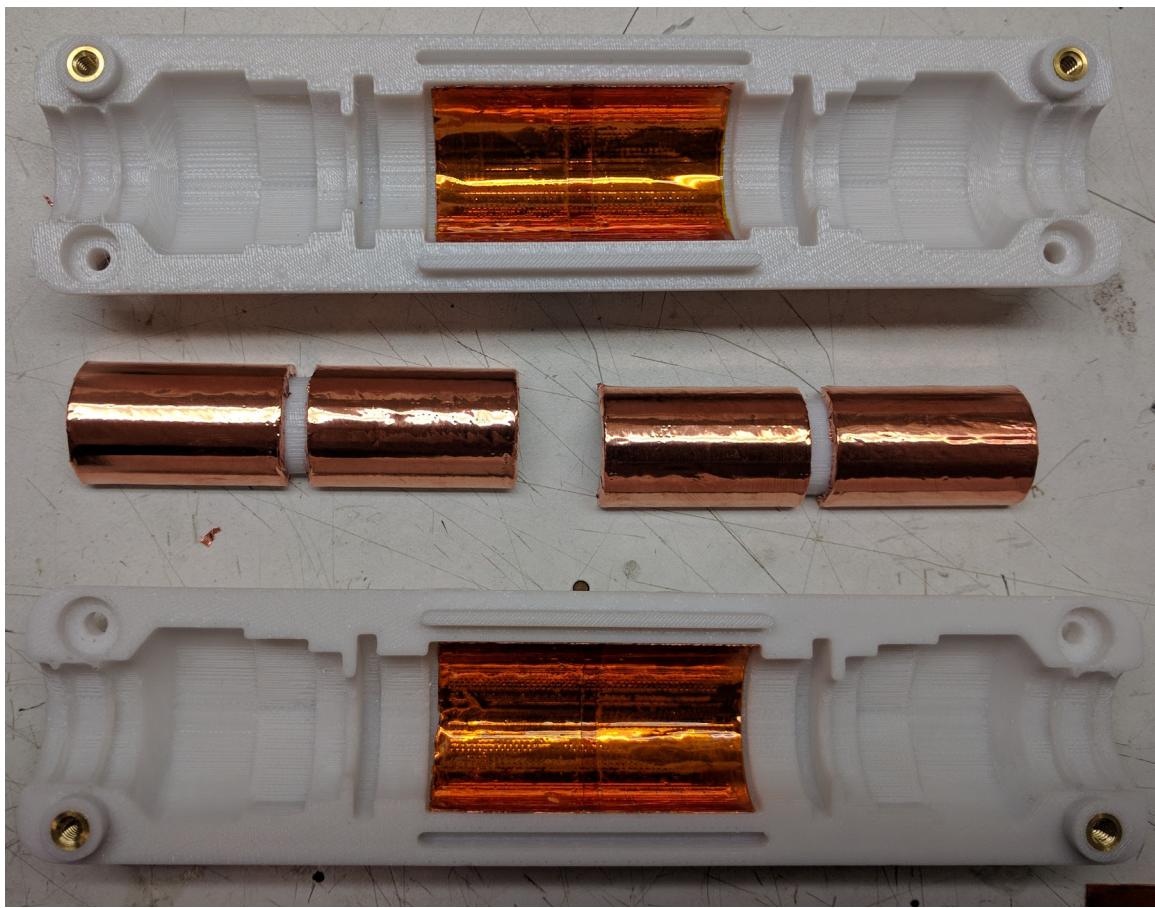


Figure 3-4: Bazooka Balun before assembly.

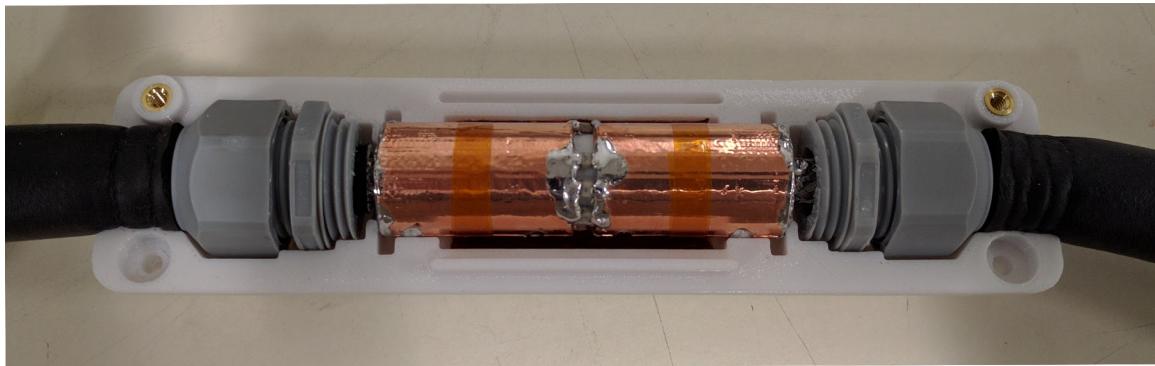


Figure 3-5: Completed bazooka balun with open enclosure.



Figure 3-6: Cable trap with current injection probes.

3.3.3 Trap Tuning

Both of the cable trap types described are narrow band, and must be properly tuned to function. This is accomplished through the use of a network analyzer and two current injection probes (fig. 3-6). Under the right measurement conditions, a prominent dip ($20dB$) in $|S_{12}|$ around the resonance frequency can be observed.

Chapter 4

Loop Elements

The same basic loop circuit, shown in figure 4-1, is duplicated 64 times to create the full array. The components appearing inside the dashed green box exist on a small FR4 circuit board termed the "feed point board." Here, I will discuss the purpose and function of each part of this circuit.

4.1 Active Detuning

The loop is a resonant circuit that is strongly coupled to the volume surrounding it. It is necessary to spoil this resonance during the high power RF transmit pulses so that excessive currents are not induced in the loop. Such unintended energy deposition could adversely affect transmit homogeneity, damage the array, or create a safety hazard. This selective detuning is achieved by switching an inductor across one of the loop capacitors, creating a parallel resonant tank that behaves as an open circuit in the loop at ω_L .

A DC bias current of about $120mA$ is injected on the line marked BIAS in figure 4-1. This bias current flows through a PIN diode, D_1 , creating an RF short and effectively switching L_{TRAP} across C_{S3} . L_{TRAP} is an adjustable air core inductor, and is hand tuned to resonate with C_{S3} at precisely ω_L . The parallel resonant circuit thus formed creates a virtual open circuit in the loop, preventing current from flowing. As soon as the bias current is removed and the diode recovers, the trap is disabled and

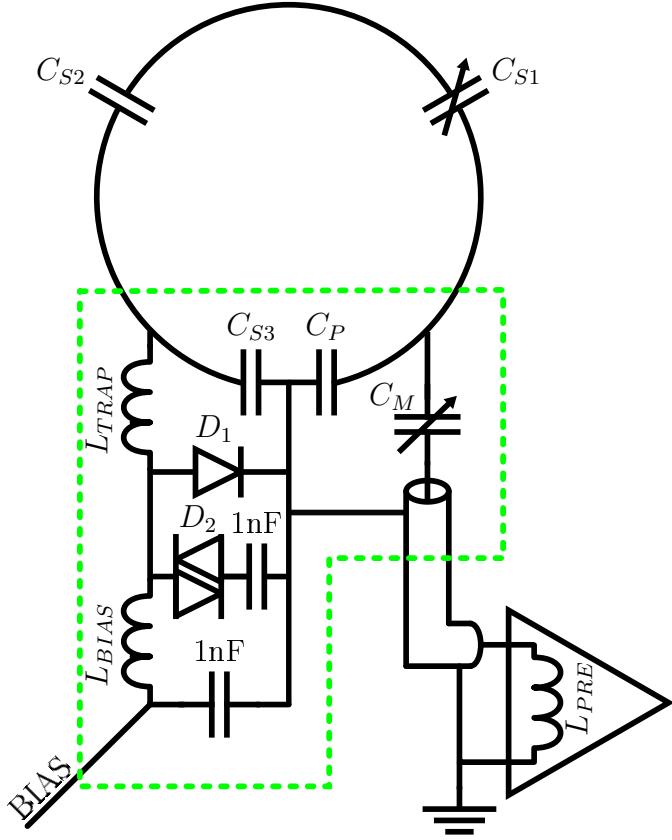


Figure 4-1: Complete loop circuit schematic

the loop once again becomes tuned.

4.2 Passive Detuning

The active detuning strategy is sufficient for assurance of image quality and protection from hardware damage, but a passive method is required to ensure patient safety in the event of an electrical failure. The crossed diode pair D_2 clamps the voltage across C_{S3} and L_{TRAP} to safe levels, passively enabling the trap if the energy stored in the loop gets too high. Other designs might also include RF fuses in the loop circuit, but the loops employed in this array are all small enough that this was not necessary.

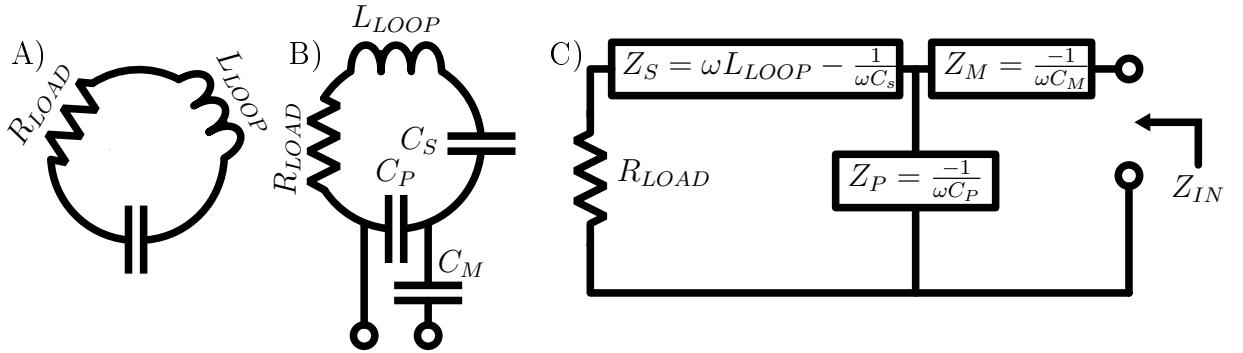


Figure 4-2: Loop circuit models.

4.3 Loop Model

The essence of the wire loop receive elements used in this array is a damped series resonant circuit, shown in figure 4-2 A. The loop has a distributed inductance by nature of its geometry, and is broken at regular intervals by discrete capacitors. Wire and component resistances and (more importantly) inductive coupling to adjacent conductive materials reduces the loop Q to a finite value. This effect is modelled by a series resistor with value $R_{LOAD} = \sqrt{\frac{L}{C}} \cdot \frac{1}{Q}$

4.4 Complete Loop Circuit

Figure 4-2 B shows the creation of an output port in the loop circuit. The total loop capacitance is split into C_P , across which the output port is formed, and C_S . A series capacitor C_M is added to one terminal of the output port. In the first part of the following analysis, grouping components values into the block impedances defined in eq. 4.1 and fig. 4-2 C results in clearer and more compact expressions, so I have made that substitution.

$$\begin{aligned}
 X_S(\omega) &= \omega L_{LOOP} - \frac{1}{\omega C_S} \\
 X_P(\omega) &= \frac{-1}{\omega C_P} \\
 X_M(\omega) &= \frac{-1}{\omega C_M}
 \end{aligned} \tag{4.1}$$

4.5 Loop Circuit Analysis

The loop circuit has an input impedance of Z_{IN} at its port, as defined in equation 4.2. This impedance can be split into its real and imaginary parts, R_{IN} and X_{IN} , shown in equations 4.3 and 4.4.

$$\begin{aligned} Z_{IN} &= (jX_p(\omega)) \parallel (jX_S(\omega) + R_{LOAD}) + jX_M(\omega) \\ &= \frac{jX_P(\omega)(jX_S(\omega) + R_{LOAD})}{j(X_P(\omega) + X_S(\omega)) + R_{LOAD}} + jX_M(\omega) \end{aligned} \quad (4.2)$$

$$R_{IN} = Re(Z_{IN}) = \frac{X_P(\omega)^2 R_{LOAD}}{R_{LOAD}^2 + (X_P(\omega) + X_S(\omega))^2} \quad (4.3)$$

$$X_{IN} = Im(Z_{IN}) = \frac{X_P(\omega)(R_{LOAD}^2 + X_S(\omega)(X_P(\omega) + X_S(\omega)))}{R_{LOAD}^2 + (X_P(\omega) + X_S(\omega))^2} + X_M(\omega) \quad (4.4)$$

4.6 Loop Component selection

4.6.1 Loop Circuit Considerations

Minimizing Preamp Noise Figure

The vendor supplied preamplifier is designed to achieve minimum noise figure when presented with a purely real 50Ω load at its input. Therefore, component values should be selected such that $R_{IN} = 50\Omega$ and $X_{IN} = 0\Omega$. Call this optimal input impedance $Z_{IN_{OPT}}$.

Preamp Decoupling

Preamp decoupling is usually achieved by resonating a capacitor in the loop (C_P in figure 4-2) with an inductor in series with one terminal of the output port (in the same position as C_M in figure 4-2) through the input of the preamplifier. In our case, however, the inductance is integrated into the preamplifier itself. I measure the inductance of the preamplifier input to be roughly $130nH$ at $123.25MHz$. The

details of the preamp topology are unavailable to me, so I simply consider it to have an impedance of $Z_{PRE} = j\omega L_{PRE}$, which is transformed to Z_{PRE}' (as shown in equation 4.5) by the short length of coaxial cable (with characteristic impedance Z_0) connecting the preamp to the loop.

$$Z_{PRE}'(\omega) = Z_0 \cdot \frac{Z_{PRE}(\omega) - jZ_0 \cdot \tan(2\pi \cdot \frac{L_{COAX}}{\lambda})}{Z_0 - jZ_{PRE}(\omega) \cdot \tan(2\pi \cdot \frac{L_{COAX}}{\lambda})} \quad (4.5)$$

$$X_{PRE}'(\omega) = Im(Z_{PRE}'(\omega)) \quad (4.6)$$

In any case, preamp decoupling is achieved when C_P , C_M , and the transformed preamp input impedance resonate together, as defined in equation 4.7.

$$X_P(\omega) + X_M(\omega) + X_{PRE}'(\omega) = 0 \quad (4.7)$$

4.6.2 Loop Resonance

I define loop resonance as occurring when $X_P + X_S = 0$, at a frequency of ω_0 (eq. 4.8). In this case, the equations for R_{IN} and X_{IN} simplify to equations 4.9 and 4.10 respectively. One can begin to see how components could be selected to set $R_{IN}|_{\omega=\omega_0} = Re(Z_{IN_{OPT}})$, but with the topology we've selected it is impossible to achieve $X_{IN}|_{\omega=\omega_0} = 0$. You could do both if you changed C_M to an inductor, but then it becomes impossible to meet the preamp decoupling condition (eq. 4.7).

$$\omega_0 = \sqrt{\frac{C_P + C_S}{C_P C_S L_{LOOP}}} \quad (4.8)$$

$$R_{IN}|_{\omega=\omega_0} = \frac{C_S L_{LOOP}}{R_{LOAD} C_P (C_P + C_S)} \quad (4.9)$$

$$X_{IN}|_{\omega=\omega_0} = -\sqrt{\frac{C_S L_{LOOP}}{C_P (C_P + C_S)}} \cdot \frac{C_M + C_P}{C_M} \quad (4.10)$$

4.6.3 Off resonance behavior

It is not necessary that the loop be tuned to resonate precisely at the frequency of interest. The position of ω_0 relative to that of the Lamor frequency ω_L is another variable that we can manipulate to achieve the desired loop circuit characteristics.

Capacitive Divider Ratio

Consider choosing C_P and C_S to achieve loop resonance at a frequency a factor α away from ω_L , so that $\omega_0 = \alpha \cdot \omega_L$. We can quickly eliminate C_S from eq. 4.8. Whatever C_P , α , and ω_L we choose will imply eq. 4.11 for C_S .

$$C_S(C_P, \alpha, \omega_L) = \frac{C_P}{C_P L_{LOOP} \alpha^2 \omega_L^2 - 1} \quad (4.11)$$

Plugging eq. 4.11 into eq. 4.3, then solving $R_{IN} = Z_{IN_{OPT}}$ for C_P , we get eq. 4.12.

$$C_P(\alpha, \omega_L) = \frac{1}{\omega_L} \sqrt{\frac{R_{LOAD}}{Z_{IN_{OPT}}(R_{LOAD}^2 + (\alpha^2 - 1)^2 \omega_L^2 L_{LOOP}^2)}} \quad (4.12)$$

Choosing α and C_M

The only remaining free parameters are α and C_M . They must be chosen to achieve purely real input impedance ($X_{IN} = 0$) and preamp decoupling ($X_P(\omega_L) + X_M(\omega_L) + X_{PRE}'(\omega_L) = 0$). Plugging in C_S and C_P from above into these two requirements results in a system of equations 4.13. Constraining α to be positive, this system has single solution: α as in eq. 4.14 and C_M as in eq. 4.15.

$$\begin{cases} \frac{-1}{\omega_L C_M} + \frac{(\alpha^2 - 1)\omega_L L_{LOOP} Z_{IN_{OPT}}}{R_{LOAD}} - \frac{1}{\omega_L C_P(\alpha, \omega_L)} = 0 \\ \frac{-1}{\omega_L C_M} + \omega_L L_{PRE} - \frac{1}{\omega_L C_P(\alpha, \omega_L)} = 0 \end{cases} \quad (4.13)$$

$$\alpha = \sqrt{1 + \frac{L_{PRE} R_{LOAD}}{L_{LOOP} Z_{IN_{OPT}}}} \quad (4.14)$$

4.6.4 Optimal Component values

With α uniquely determined, C_M , C_P , and C_S are each fully constrained. Our final component value formulas are shown in eq. 4.15.

$$\begin{aligned} C_M &= \frac{1}{\omega_L} \cdot \frac{1}{\omega_L L_{PRE} - \sqrt{\frac{R_{LOAD}}{Z_{INOPT}}(\omega_L^2 L_{PRE}^2 + Z_{INOPT}^2)}} \\ C_P &= \frac{1}{\omega_L} \cdot \frac{1}{\sqrt{\frac{R_{LOAD}}{Z_{INOPT}}(\omega_L^2 L_{PRE}^2 + Z_{INOPT}^2)}} \\ C_S &= \frac{1}{\omega_L} \cdot \frac{1}{\omega_L(L_{PRE}\frac{R_{LOAD}}{Z_{INOPT}} + L_{LOOP}) - \sqrt{\frac{R_{LOAD}}{Z_{INOPT}}(\omega_L^2 L_{PRE}^2 + Z_{INOPT}^2)}} \end{aligned} \quad (4.15)$$

4.6.5 Verifying Optimal Component Values

Figure 4-3 illustrates the success of this component selection strategy in simultaneously achieving optimum input impedance and preamp decoupling. The impedance plots shown are based on estimated parameters of a loop in the belly panel. Numerical values for this simulation are summarized in tables 4.1 and 4.2.

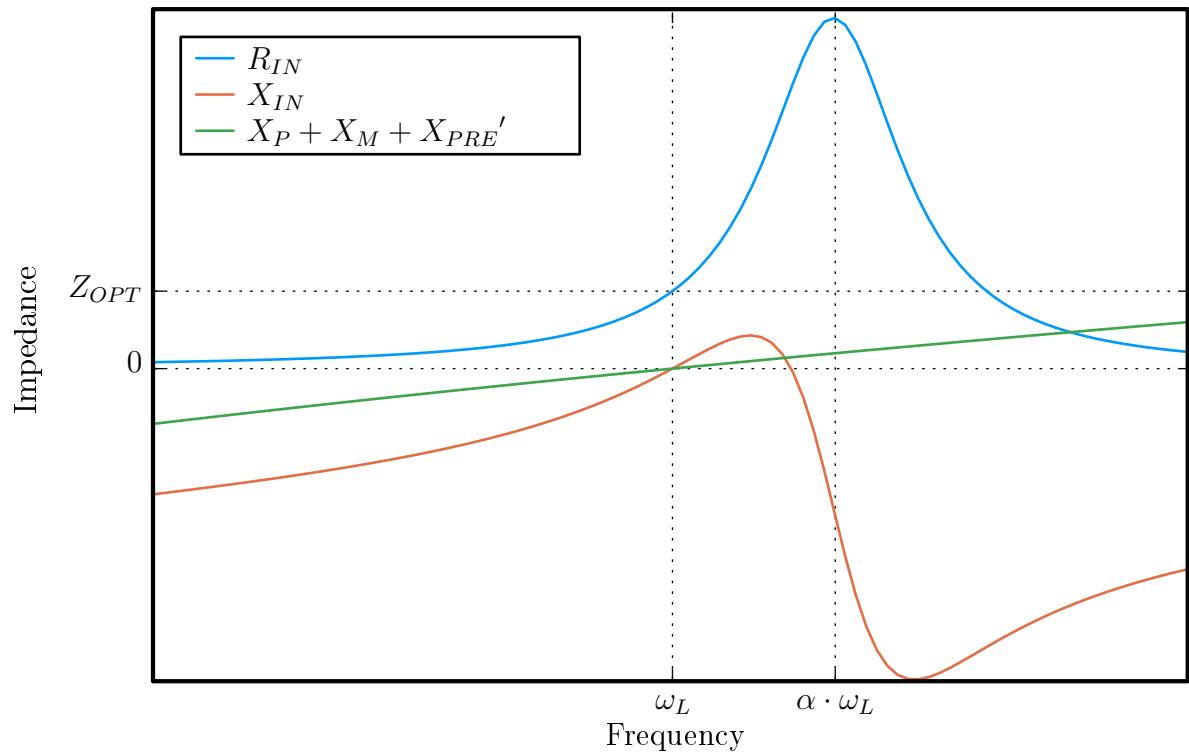


Figure 4-3: Loop impedances vs. frequency with optimal component values.

Table 4.1: Loop Simulation Parameters

Parameter	Value
R_{LOAD}	10Ω
L_{LOOP}	$247nH$
L_{PRE}	$130nH$
Z_{INOPT}	50Ω
ω_L	$123.25MHz$

Table 4.2: Loop Simulation Component Values

Parameter	Value
C_M	$25.8pF$
C_P	$25.8pF$
C_S	$8.0pF$
α	1.051

Chapter 5

Testing

The aim of this project was to create a custom coil that performs better than existing arrays in a particular application. Our primary means of evaluating relative performance is direct comparison of two related performance metrics: SNR maps and SENSE geometry factor (g-factor) maps. A brief discussion of each follows. For a complete treatment, see the original SENSE paper: [3].

5.1 Signal to Noise Ratio Maps

The MR signal to noise ratio provided by any coil or coil array varies as a function of space. A heatmap of SNR in a given plane is a useful visual tool that can be used to judge whether a coil is well suited to imaging in a particular region of interest such as the fetal brain or placenta. A SNR map is easy to generate for a single coil. One can simply run an imaging sequence with intrincicly high SNR twice; once with an initial RF excitation and once without. The first sequence should produce an image that is dominated by the MR signal, and the second sequence produces a noise only image. A SNR map in conventionally defined SNR units is obtained by dividing the first image by the standard deviation of the noise only image.

Generating SNR maps for multi coil arrays is less straightforward, and depends on the method used to combine data from individual elements. The Roemer paper [5] describes an optimal way of combining array coil data in the spatial domain that

results in maximum SNR and normalized noise intensity in every voxel of the resulting image. First, a complete image is acquired and reconstructed from every element in the array. Next, a sample of pure noise data is acquired to generate a channel noise covariance matrix Ψ , of which a single element Psi_{ij} is the noise covariance between receivers i and j . Next, the individual coil images are combined on a voxel by voxel basis. For a single voxel, arrange the values S_i of that voxel in each of the individual coil images in a vector S . Similarly, arrange the sensitivities of each coil to the voxel under consideration in a vector C . The matrix equation for the voxel intensity in the optimal SNR uniform noise image is then 5.1. If the individual coil images have sufficiently high SNR, then S serves as a good approximation of C , and equation simplifies to 5.2. If it is assumed that there is no noise correlation between distinct channels and that all channels are identically loaded, Ψ becomes proportional to the identity matrix, and the optimal SNR formula simplifies to 5.3. This is equivalent to summing the squared magnitudes of the uncombined images, then taking the square root of the result.

$$I_{OPT} = \frac{C^H \Psi^{-1} S}{\sqrt{C^H \Psi^{-1} C}} \quad (5.1)$$

$$I_{COV} = \sqrt{S^H \Psi^{-1} S} \quad (5.2)$$

$$I_{RSOS} = \sqrt{S^H S} \quad (5.3)$$

TODO:SNR equations

5.2 SENSE Geometry Factor

5.2.1 k-space sampling for the 2DFT

The basic Fourier abstraction used in traditional 2D MRI with cartesian k-space sampling illuminates a fundamental constraint on imaging speed: k-space traversal speed.

Sampling Constraints

The spatial extents of an image dictate the spectral spacing of samples that must be acquired to encode it with the DFT. [2] .In order to 2D Fourier encode an image of width FOV_x and height FOV_y , k-space samples must be spaced $\frac{1}{FOV_X}$ apart in the k_x direction and $\frac{1}{FOV_Y}$ apart in the k_y , direction, as defined in eq. 5.4.

$$\begin{aligned} FOV_x z &= \frac{1}{\delta k_x} \\ FOV_y &= \frac{1}{\delta k_y} \end{aligned} \quad (5.4)$$

The spatial resolution of an image dictates the extents of spectral data that must be acquired to encode it with the DFT. In order to 2D Fourier encode an image with voxels δ_x wide and δ_y tall, data must be sampled over a period of approximately $\frac{1}{\delta_x}$ in the k_x direction and $\frac{1}{\delta_x}$ in the k_x direction, as defined in eq. 5.5.

$$\begin{aligned} \delta_x &\approx \frac{1}{2k_{xmax}} \\ \delta_y &\approx \frac{1}{2k_{ymax}} \end{aligned} \quad (5.5)$$

It is clear that the number k-space samples needed to resolve an image grows linearly with both FOV and voxel density, and that the maximum extents of those samples in k-space increases linearly with voxel density. K-space is sampled by traversing a continuous path that sequentially visits the coordinates of each sample. The maximum speed of k-space traversal is fundamentally limited by patient safety considerations and technological limitations. limitation. So, for a given maximum spread and optimum path, there is a minimum acquisition time for a fully sampled 2DFT sequence with a given FOV and spatial resolution.

Cartesian Undersampling

An imaging sequence can be accelerated by skipping some points in k-space, then attempting by some means to reconstruct a complete image from incomplete k-space data. In the case of cartesian sampling for the 2DFT, a natural strategy is to regularly

skip entire lines of k-space data in one dimension.[3], for example acquiring every other line ($R=2$) or every third line ($R=3$). The effect of this regular undersampling strategy is to effectively increase δk by a factor of R , and to accordingly decrease FOV by the same factor of R . This causes parts of the object being imaged that lie outside of the reduced FOV to wrap around the edges of that FOV and alias onto other voxel positions.

SENSE

The Pruessmann paper [3] introduced the strategy of "Sensitivity Encoding" as a means of undoing the aliasing induced by undersampling. In an array coil, different receive elements have different spatial sensitivity profiles. These varying sensitivities provide different "views" of the same aliased image, and this extra information is used to unfold the aliased image on a pixel by pixel basis.

Consider an array with n_C individual elements, each with a unique view of a voxel location that, in the reduced FOV image, represents a superposition of n_P physical voxel locations. A sensitivity matrix S is constructed to describe the sensitivity of each receive element to each of the voxel positions that are aliased into a single pixel in the final image. An individual element $S_{\gamma,\rho}$ in this matrix represents the sensitivity of receive element number γ to superimposed pixel ρ . The values of the voxel in the reduced FOV images from each receive element are arranged in a vector of length n_C : \vec{a} . Similar to in the previous section, a $n_C \times n_C$ receiver noise covariance matrix. The unfolding matrix is then U (eq. 5.6), and the vector of image values in the n_p voxels of the unaliased image are estimated by $\vec{v} = U\vec{a}$. This unfolding process is repeated for every voxel in the reduced FOV image.

$$U = (S^H \Psi^{-1} S)^{-1} S^H \Psi^{-1} \quad (5.6)$$

SENSE g-factor

By accelerating an image acquisition by a factor of R , we expect that the SNR of the resulting image must correspondingly decrease by a factor of $\frac{1}{\sqrt{R}}$ [2]. Usually,

though, imperfect conditioning of the sensitivity matrix results in a steeper SNR penalty. The extent to which SENSE underperforms the best case SNR penalty is characterized by the geometry factor, or g-factor, defined in eq. 5.7. The g-factor varies as a function of space, and is defined for each voxel in the full FOV image. It is called the geometry factor because it depends largely on the geometry of the receive array. With more independent views of an aliased pixel are available, a higher acceleration factor can be attempted without poor conditioning amplifying noise to an unacceptable degree.

$$g_{SENSE} = \frac{1}{\sqrt{R}} \cdot \frac{SNR_{FULL}}{SNR_{ACCEL}} \quad (5.7)$$

Plots of 2D SENSE g-factor maps in a given slice are a useful graphical tool for assessing the ability of an array to support a given acceleration factor along a particular dimension (or, along two dimensions simultaneously.) SENSE g-factor is widely used to compare the acceleration capability of different coil arrays because it is straightforward to compute and gives insights into the fundamental ability of an array to enable acceleration using any method. Still, it is important to note that unique formulations of g-factor have developed for other acceleration methods, such as SMASH and GRAPPA [1].

Chapter 6

Methods

6.1 MRI Data Acquisition and Reconstruction

Images of the pregnant abdominal phantom were acquired for using both the 64 channel fetal coil and the standard combination of 16 channels from a 32 channel spine array and all channels from an 18 channel flexible body array. Three orthogonal slices (transverse, coronal, and sagittal) intersecting the fetal brain compartment were carefully duplicated using both array configurations. An extremely high SNR PD weighted 2DGRE sequence ($TR = 3500ms, TE = 4ms, FA = 45^\circ, FOV = 400mm, \delta \approx 2mm \times 2mm \times 7mm, BW = 180Hz/px$) was chosen so that each of the uncombined coil images has decent SNR (> 20) in the deep central region of the fetal brain compartment, and thus can be taken as an accurate approximation of a coil sensitivity map [5]. The same sequence was run with the reference TX voltage set to 0V to acquire noise-only data for the generation of a noise covariance matrix Ψ . Data were acquired on a 3T Magnetom Skyra System (Siemens Healthcare, Erlangen, Germany).

Covariance weighted SNR maps and SENSE g-factor maps were computed offline using the resulting raw data. For the fetal coil, single channel SNR maps were generated by dividing each of the 64 uncombined coil images by the standard deviation of a corresponding noise only image. The mean value of each single channel SNR map was computed inside an ROI ($A = 29$ voxels) in the fetal brain region of the

anthropomorphic phantom as a means of assessing the relative importance of each component in the array geometry.

6.2 Bench Tests

6.2.1 Intercoil Coupling and Reflection Coefficient Measurements

A network analyzer connected directly to loop output ports was used to measure coupling between neighboring coil elements (S_{12}), and to measure individual coil output reflection coefficients (S_{11}). For each of these tests, the output power of the network analyzer was reduced to -25dBm and the coil was appropriately loaded by a test phantom. This test configuration was used during the iterative geometric decoupling adjustment process, where the loops are manually bent and reconfigured to minimize neighbor-to-neighbor coupling.

6.2.2 Loop Detuning and Preamp Decoupling Verification

The active detune capability and preamp decoupling performance were tuned and characterized using a pair of decoupled ($S_{12} < 70dB$) inductive probes loosely coupled to the loop under test. In this arrangement, the S_{12} measurement between the two probes is directly proportional to the current flowing in the loop [4]. Both the active detune capability and preamplifier decoupling strategy work by introducing a second resonance near the loop resonance frequency, which "splits" the loop resonance into two peaks above and below the initial resonance frequency. The null between these peaks is moved to ω_L by adjustment of a tunable component. For the active detune strategy, this tunable component is an adjustable air-core inductor (L_{TRAP} in fig. 4-1). For preamp decoupling, it is a trim capacitor (C_M in fig. 4-1).

Chapter 7

Results

7.1 Covariance Weighted SNR Maps

Covariance weighted SNR maps for three perpendicular slices chosen to intersect the fetal brain compartment are shown in figs. 7-1, 7-2, and 7-3. In each cross section, it can be seen that the fetal array provides greatly increased SNR in the periphery of the phantom, but only narrowly outperforms the standard array configuration in the deep central region where the fetus is actually located. In this particular dataset, SNR was improved by approximately 5% inside the fetal brain compartment in each of the three slices.

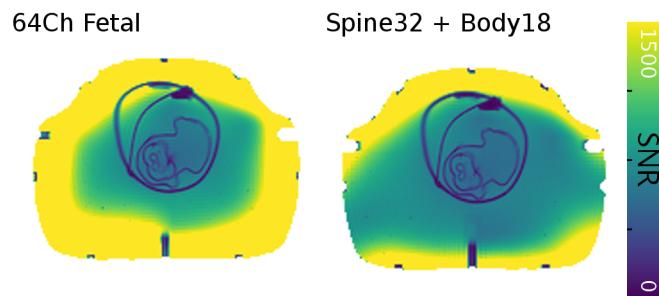


Figure 7-1: Comparative Covariance Weighted SNR Maps, Transverse Slice Through Fetal Phantom Brain.

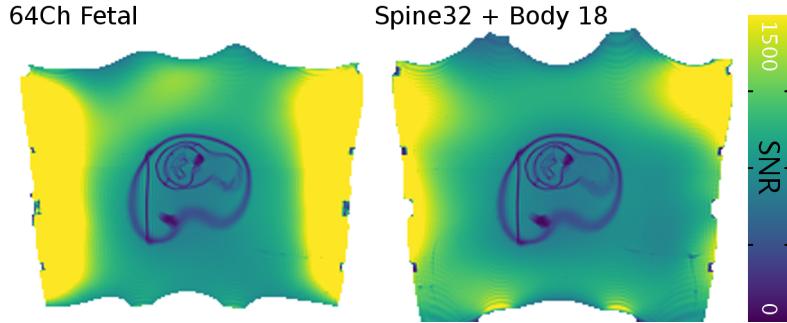


Figure 7-2: Comparative Covariance Weighted SNR Maps, Coronal Slice Through Fetal Phantom Brain.

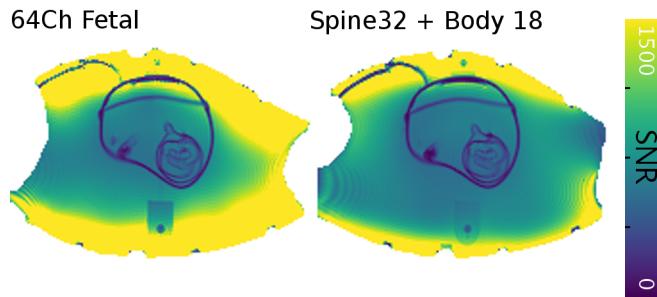


Figure 7-3: Comparative Covariance Weighted SNR Maps, Sagittal Slice Through Fetal Phantom Brain.

7.2 Inverse G-Factor Maps

As compared to the standard combination of the 32 channel spine array and 18 channel flexible body array, the 64 channel fetal coil allows increase in SENSE acceleration factor from four to five in the right-left direction (figs. 7-4, 7-6) and 3 to 4 in the head-foot direction (figs. 7-7, 7-8) while maintaining acceptably low noise amplification levels. Both array configurations have poor acceleration capability in the anterior-posterior direction (figs. 7-5, 7-9). Note that in order to increase contrast in the relevant range, the color scale on these maps goes from 0.5 to 1, not 0 to 1.

Figure 7-10 shows inverse SENSE g-factor maps for 2D acceleration in the head-foot and left-right directions, comparing array performance at $R = (3, 4)$ and $R = (4, 5)$. This comparison was chosen to highlight the best case improvement in acceleration capability provided by the fetal coil. Inside a large central ROI covering the entire fetus, the fetal coil maintains $g \leq 1.5$ with $R = 4, 5$ while the product array only achieves $g \leq 3.9$. In the same ROI, they have mean inverse g-factors ($1/g$) of 0.82

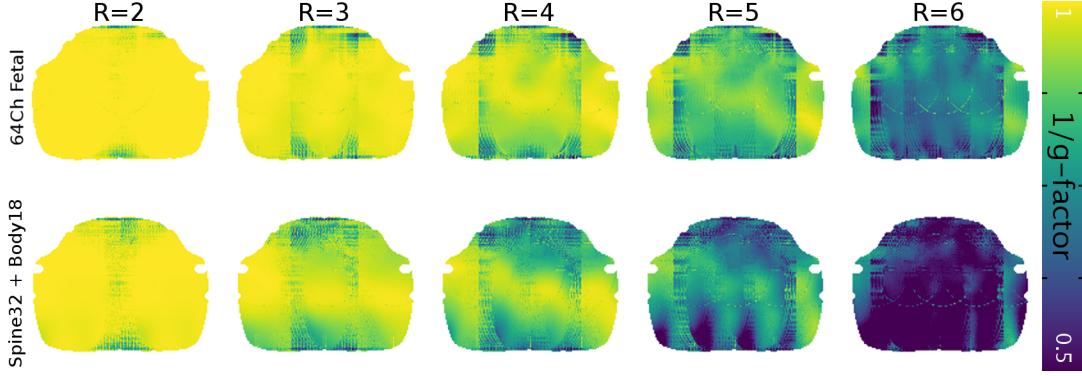


Figure 7-4: Comparative Inverse SENSE G-Factor Maps, Transverse Slice Through Fetal Phantom Brain, Acceleration in Right-Left Direction.

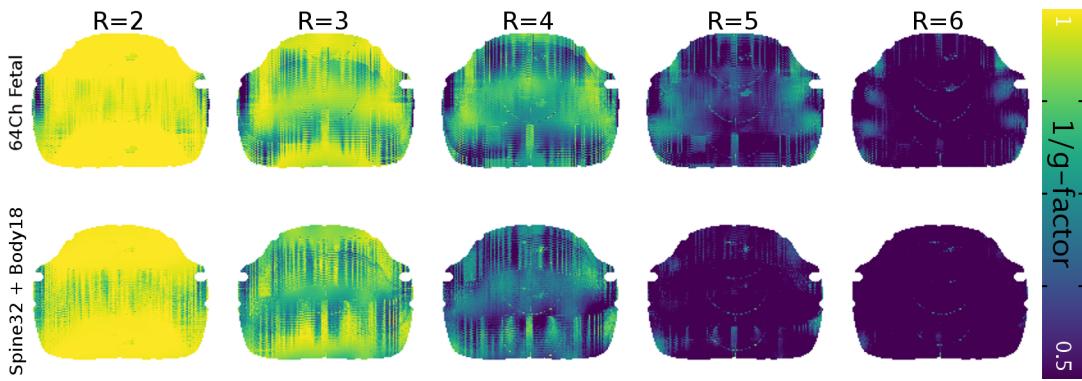


Figure 7-5: Comparative Inverse SENSE G-Factor Maps, Transverse Slice Through Fetal Phantom Brain, Acceleration in Anterior-Posterior Direction.

and 0.43, respectively. Roughly speaking, the fetal coil has noise amplification levels at $R = (4, 5)$ that are comparable to the standard array configuration at $R = (3, 4)$. This represents a 67% increase in overall acceleration factor.

7.3 Noise Matrices

Figure 7-11 shows the absolute value of a noise covariance matrix Ψ calculated from this dataset. Figure 7-12 shows the same data normalized along the diagonal so that the element with indices j, k is the correlation coefficient for channels i and k . The correlation coefficient is equal to 1 when $j = k$.

The average off diagonal correlation coefficient is 0.051, and the maximum is 0.12. Looking at the correlation coefficient matrix, several clearly defined regions of

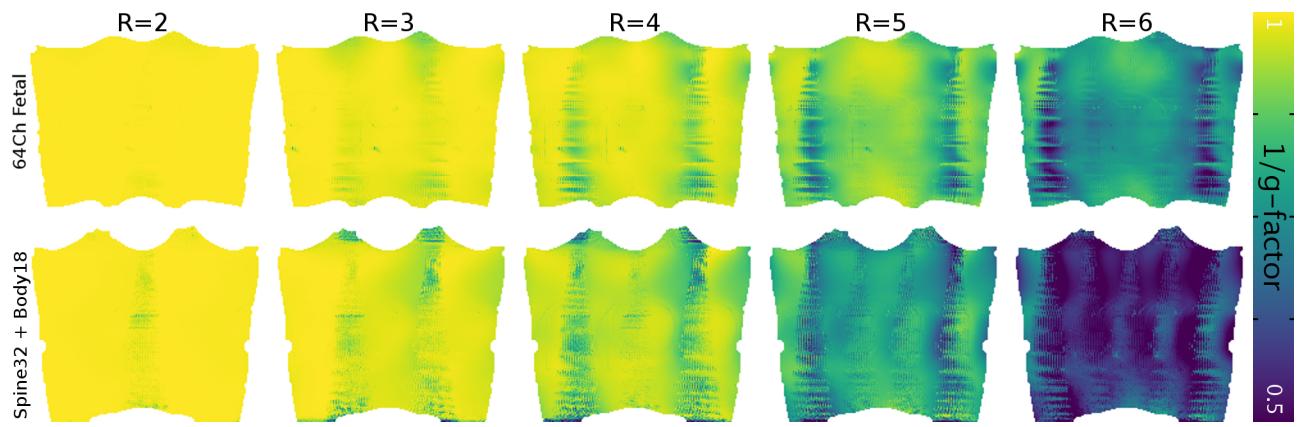


Figure 7-6: Comparative Inverse SENSE G-Factor Maps, Coronal Slice Through Fetal Phantom Brain, Acceleration in Right-Left Direction.

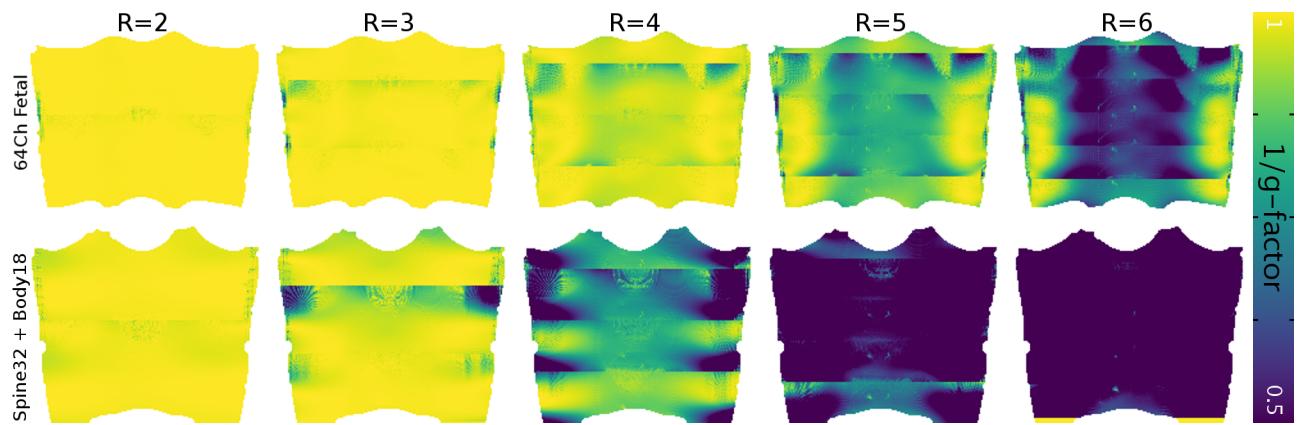


Figure 7-7: Comparative Inverse SENSE G-Factor Maps, Coronal Slice Through Fetal Phantom Brain, Acceleration in Head-Foot Direction.

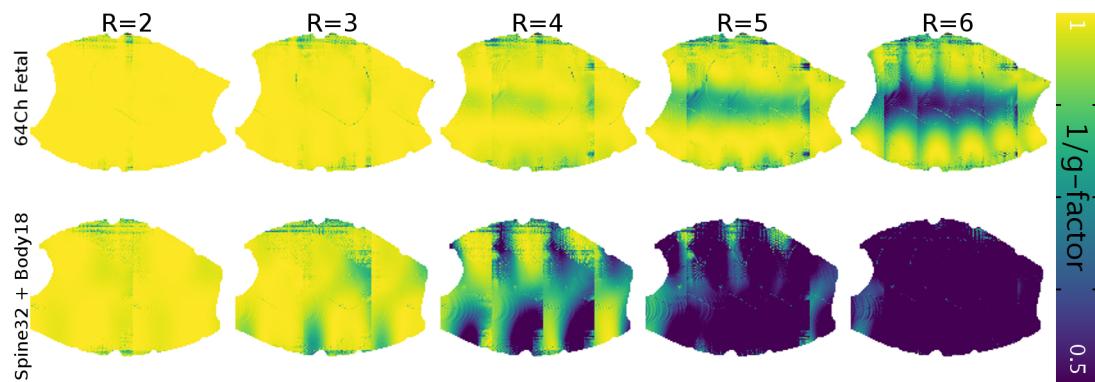


Figure 7-8: Comparative Inverse SENSE G-Factor Maps, Sagittal Slice Through Fetal Phantom Brain, Acceleration in Head-Foot Direction.

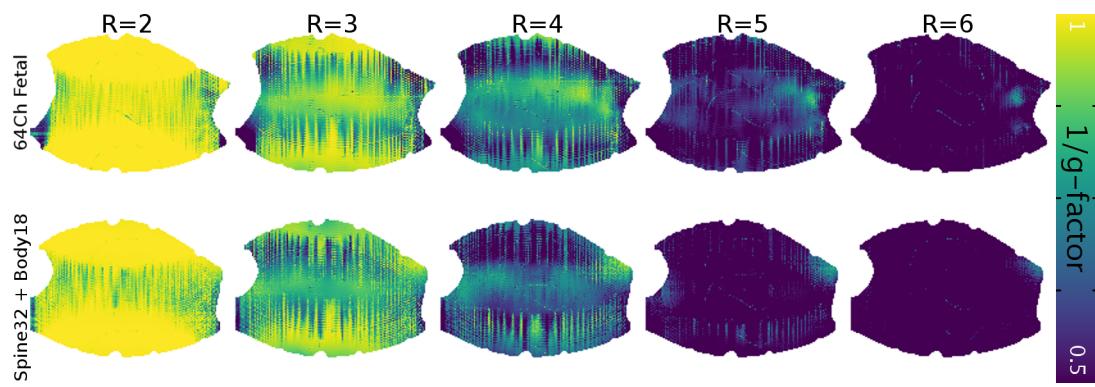


Figure 7-9: Comparative Inverse SENSE G-Factor Maps, Sagittal Slice Through Fetal Phantom Brain, Acceleration in Anterior-Posterior Direction.

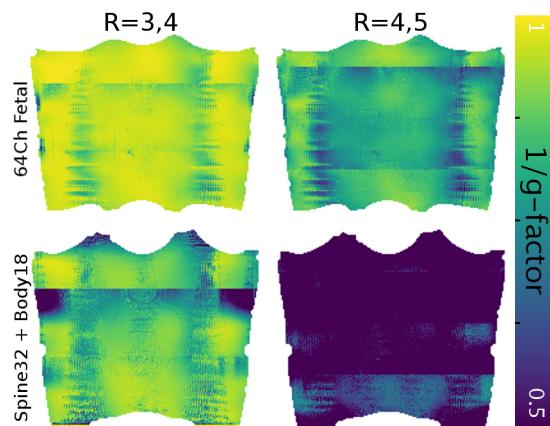


Figure 7-10: Comparative Inverse SENSE G-Factor Maps, V Coronal Slice Through Fetal Phantom Brain, Acceleration in Head-Foot, Right-Left Directions.

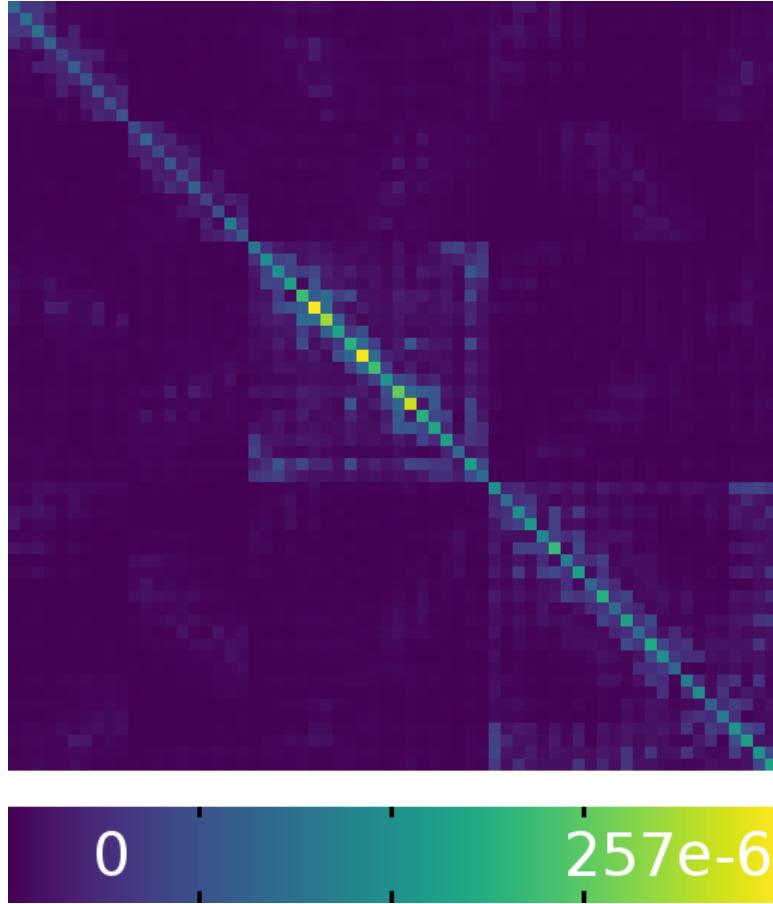


Figure 7-11: Absolute value of noise covariance matrix ($|\Psi|$).

moderate correlation are apparent, with almost no correlation between different regions. The groupings follow the separation of elements into different array panels. From top left to bottom right, we see channels from the right side wing, left side wing, abdomen panel, and back panel.

7.4 Per-Element SNR

Figure 7-13 is a 1:4 scale diagram of the actual loop geometry used in the fetal array. Displayed inside each loop is the mean SNR of that channel inside the fetal brain ROI. It can be seen that elements in the back panel contributed most to overall SNR in the fetal brain compartment, followed by the belly panel and side wings.

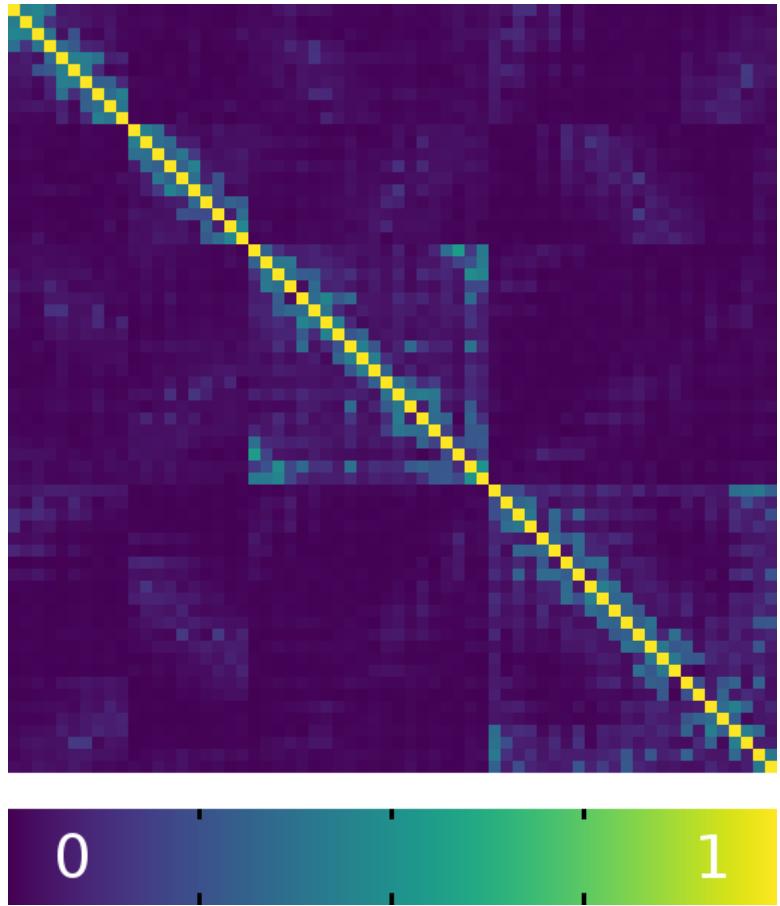


Figure 7-12: Absolute value of inter-channel noise correlation coefficients ($|\sqrt{\text{diag}(\Psi)}^{-1} \cdot \Psi \cdot \sqrt{\text{diag}(\Psi)}|$).

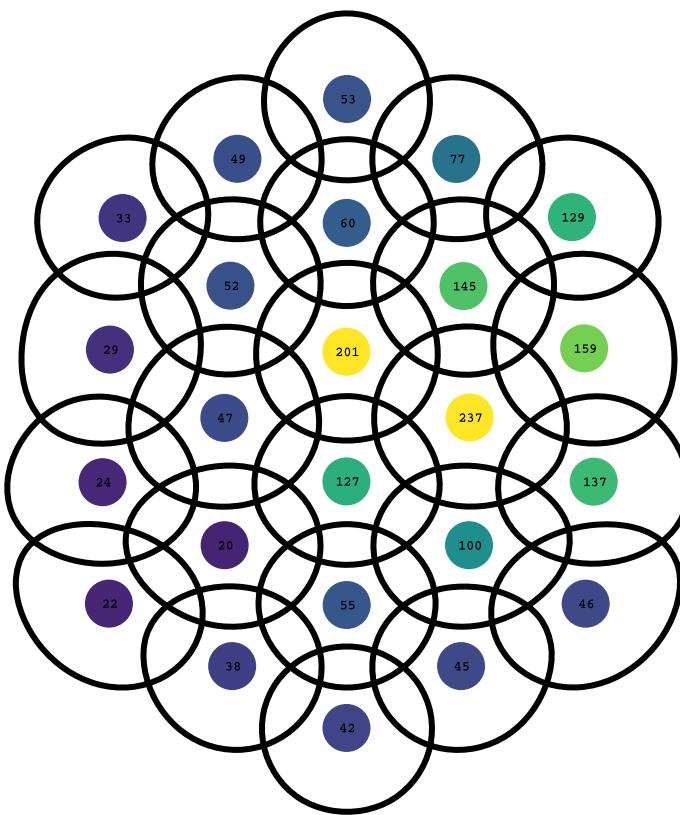
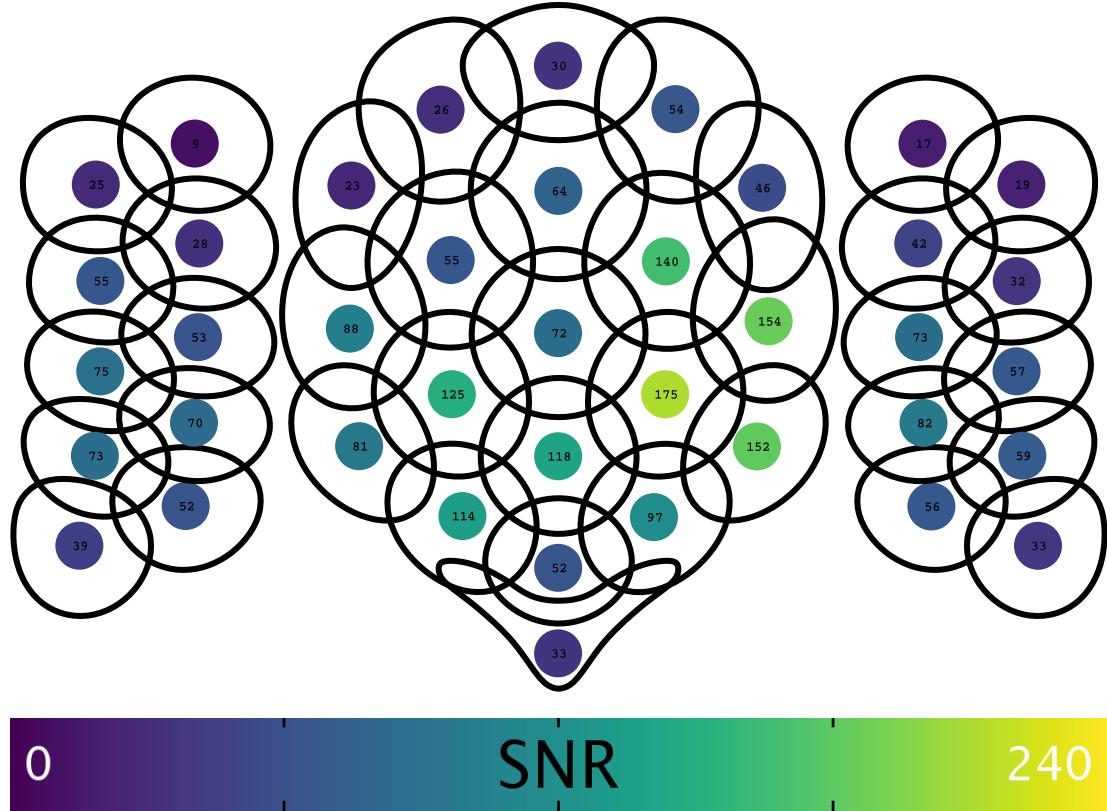


Figure 7-13: Mean Single Element SNR values Inside the Fetal Phantom Brain
(Top:Abdomen Panel and Side Wings, Bottom: Back panel)

Chapter 8

Discussion

The modest SNR improvement seen in unaccelerated imaging is likely attributed to the deep (nearly central) location of the fetal head where coil arrays with more than 16 elements already approach the ultimate SNR available [6]. Nonetheless, because the SNR is achieved with array elements with higher spatial frequency sensitivity profiles, there is an improvement in acceleration capability.

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