



**KTH Electrical Engineering**

MEMS tunable integrated polarization  
rotator for communication and sensing

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# 1

## Chapter 1

# Introduction

## 1.1 Optical communication

Communication and collective thinking are the key to the development of human civilization. This development is driven by data - “The new oil of this digital era”. With the advent of Internet of Things (IoT), there has been a huge surge in data traffic all over the world. It has been estimated that by 2020 there will be 26 billion connected devices [1], and all devices that can be connected will be connected. Ericsson’s mobility report [2] estimates that 70% of world’s population will use smart-phones by 2020 and 90% of the world’s population over 6 years old will have a mobile phone by 2020. Today, only about 40% [3] of the world’s population use the internet. With more users and different connected devices, eventually data traffic is poised to grow exponentially, as shown in Fig. 1.1, as per Ericsson [4].

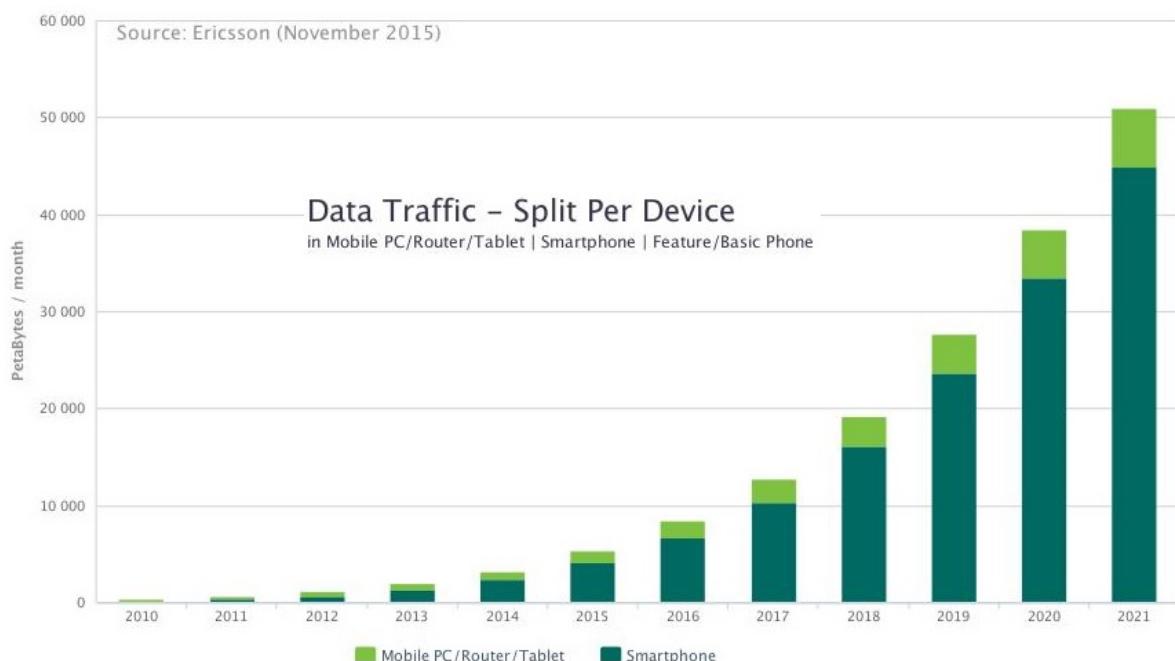


Figure 1.1: Data traffic growth forecast by 2020, as per Ericsson, generated using [4]

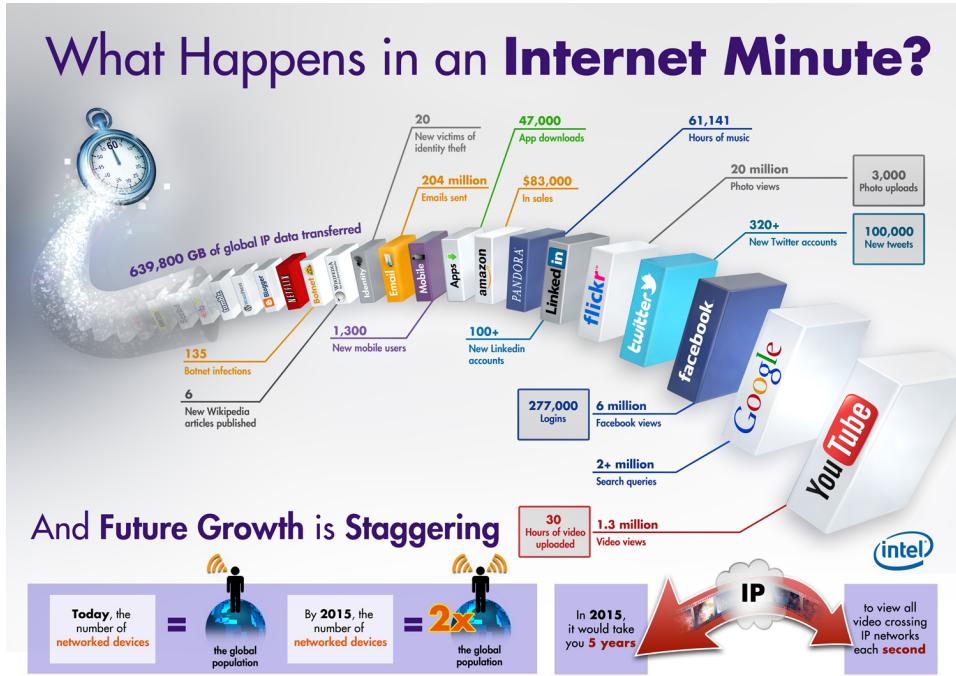


Figure 1.2: What happens on internet per minute [5]

Currently, as illustrated in Fig. 1.2, huge data is processed per minute due to different Information and communication technology (ICT) services. Eventually, as more and more people use these different ICT services on different devices, this data growth will be higher than ever. In consequence, the telecommunications industry has started moving towards IP Multimedia Subsystem (IMS) core networks, which is transition towards full IP based networks. So how is this traffic managed? The answer is the optical fiber, which serves as the backbone of all the communication systems. Optical fiber is chosen over previously used copper cables for the following reasons:

- Fiber provides more bandwidth than copper and has standardized performance up to 100 Gbps and beyond, with very low power consumption.
  - Fiber is less susceptible to temperature fluctuations than copper and can be submerged in water for intercontinental long distance communication. Unlike copper, it's immune to Electromagnetic (EM) interference.
  - It doesn't radiate signals and is extremely difficult to tap, which provides better security than copper cables.
  - Fiber optic transmission results in less attenuation (losses) than copper cables.
- Less than copper... verify

## 1.2 Silicon photonics

The performance of optical fiber networks is remarkable and it is this backbone which gives us a great user experience. The current internet architecture has already pushed the optical fiber to the network edges and the trend is to push it as closer to the processor as possible. This has already opened up a new trend of “siliconizing photonics” [6], which arose from the decades of research from microelectronics industry.

The electronics industry has pushed the boundaries of the processing speed of Integrated circuit(s) (IC) according to Moore’s Law. Until recently, exponential increases in the speed, efficiency, and processing power of conventional electronic devices were achieved largely through the downscaling and clustering of components on a chip. However, this trend toward miniaturization has yielded unwanted effects in the form of significant increases in noise, power consumption, signal propagation delay and aggravates already to serious thermal management problems. Alternatively, the wires can be made thicker, but then the packing density will be inefficient. As a result, traditional microelectronics will soon fall short of meeting market needs, inhibited by the thermal and bandwidth bottlenecks inherent in copper wiring. Intel processor speed and bus speed comparison shows that although we have achieved good processing speed, the interconnects always find difficulty in catching up with the processing speed [7]. Annual global data center IP traffic will reach 10.4 zettabytes (863 exabytes per month) by the end of 2019, up from 3.4 zettabytes per year (287 exabytes per month) in 2014 [8]. Think of a server rack in a data center processing an average of this huge data per second, where interconnects between multiple processors in the server rack add up to a significant bottleneck. These bottlenecks can be overcome by substituting copper with optical interconnects using the current technology, which can also operate at low power and better efficiency. In addition optical interconnects can also reduce heat dissipation, switching and transmission of electrical signals.

Although silicon is the material of choice for electronics, only from late 1980s silicon is being considered as a practical option for Optoelectronic integrated circuit (OEIC) solutions. Silicon has many properties that make it a good material for optics. First of all, the band gap of silicon ( $\sim 1.1 \text{ eV}$ ) is such that the material is transparent to wavelengths commonly used for optical communication ( $\sim 1.3 \mu\text{m}-1.6 \mu\text{m}$ ). Moreover, one can use standard Complementary metal-oxide semiconductor (CMOS) processing techniques to sculpt optical waveguides onto the silicon surface. Similar to an optical fiber, these waveguides can be used to confine and direct light as it passes through the silicon [9] using total internal reflection. Due to the wavelengths typically used for optical transport and silicon’s high index of refraction, the feature sizes needed for processing these silicon waveguides are on the order of  $0.5 \mu\text{m}-1 \mu\text{m}$ . This makes silicon excellent for miniaturization of optical components. The fabrication and lithography requirements needed to process waveguides with these sizes exist today. Finally, it is CMOS-compatible, making it possible to process monolithic optical devices, which could bring new levels of performance, functionality, power and size reduction, all at a lower cost.

Today silicon photonics is a new approach to make miniaturized optical devices that use light to move huge amounts of data at very high speeds with extremely low power

over a thin optical fiber rather than using electrical signals over a copper wire. Since already a large capital investment has been done on perfecting the current fabrication technology and infrastructure, engineers are working on creating monolithic design of integrated circuits which will use light instead of electric signals [10]. Research institutes and industry, are trying to bridge this gap by creating highly integrated photonic and electronic components that combine the functionality of conventional CMOS circuits with the significantly enhanced performance of photonic solutions. Various kinds of silicon photonic devices, such as switches [11, 12, 13, 14], modulators [15, 16], photo-detectors [17, 18], delay lines [19, 20], sensors [21, 22, 23] etc. have been reported till date. This leads to a booming silicon photonics market, which is estimated to grow to 700 million USD by 2024 [24, 25] with a Compound annual growth rate (CAGR) of 38%.

### **1.3 Motivation for MEMS tunable polarization rotator**

To keep up with bandwidth requirements using existing network infrastructure, spatial-division multiplexing technique [26] is being contemplated, which uses multimode transmission. However, simply connecting the end of such fibers to an OEIC is far more complicated than standard fibers, because much more mechanical precision is required. Great care has to be taken to make sure light goes in exactly as intended [27]. Moreover, all photonic devices based on silicon waveguides are sensitive to polarization due to large structural birefringence, which induces substantial polarization dependent loss (PDL), polarization mode dispersion (PMD), and other polarization dependent wavelength characteristics ( $PD\lambda$ ), limiting their usability. Also, in a complex OEIC system, polarization is a major issue because power can be exchanged between the polarization states in the presence of junctions, tapers, slanted sidewalls, bends, or other discontinuities. Therefore, sometimes, it is necessary to have a fixed degree of polarization state, and it may also be necessary to rotate an incoming polarization state.

To overcome these challenges, polarization rotator (PR) is engineered on silicon for OEIC and various designs have already been demonstrated [28, 29, 30, 31, 32, 33, 34]. The main working principle of these proposed solutions is introducing asymmetry in the waveguide structure. However, in some cases, the designs [35], if used in commercial applications for miniature interconnects, would incur inefficient packing density since too much space is required to achieve high and robust tuning. Apart from that there might also be thermo-optic cross-talk problem which might change phase of the wave in other waveguides in high compact density environment as silicon is highly susceptible to thermal changes [36]. Also, a Tunable polarization rotator (TPR) has been reported which works on the principle of Berry's phase, a quantum-mechanical phenomenon of purely topological origin [37]. For PR, the design uses out-of-plane ring cavity which inherits the narrow band spectral features of ring resonator limiting the bandwidth. Phase tuning is achieved through thermo-optic effect which has its limitations. The general goal of the thesis work is to realize an efficient TPR using Microelectromechanical systems (MEMS) in C and L bands, at low power, with high precision and accuracy.

## **1.4 Objectives of the thesis**

**Main objective:** To design and fabricate low power TPR based on MEMS tuning.

**Sub objectives:** The areas which will be addressed are:

- Feasibility of the idea and the strategy to design the TPR.
- Design and simulation of the device.
- Fabrication and characterization of the MEMS TPR.

## **1.5 Outline of this thesis**

The outline of the thesis is as follows: Background, motivation and the research questions being addressed, is discussed in Chapter 1. In Chapter 2, the current state of art for the available solution is discussed along with the background literature required. Here, also the working principle of the current available design are explained along with the areas which can be improved. Chapter 3 discusses about the design of the final system and the results obtained about the simulation setup. In Chapter 4, documentation about the fabricated design is provided along with currently available standard fabrication technologies. Results and characterization are an important part of the work, which is discussed in Chapter 5. Finally, Chapter 6 and 7 discusses about the future work possibilities respectively along with the known limitations and conclusion of the system if any.

# 2

## Chapter 2

# State of the art

To understand the working principles of PR it is important to look into the basic concepts of waveguides and the mathematics behind the propagation of EM waves. It is also necessary to understand tuning of optical waveguides using different mechanisms to achieve optical PR. Finally, the integrated PRs found in the recent literature and their underlying concepts are discussed.

## 2.1 Optical waveguide theory

Light can travel through dielectric waveguide. To comprehend the situation we need to look at the physical properties of light and waveguides. The basic understanding of Maxwell's equations is required. Maxwell combined the electric and magnetic fields in a wave equation. Since we need a formal definition of the different state of polarization (SOP), described using Jones calculus. Moreover, the rotation from one SOP to another, can be defined formally on the Poincaré sphere.

### 2.1.1 Maxwell's equations

Wave is a disturbance that propagates through a medium. Waves transfer both energy and momentum, without transferring any mass. EM radiation is the radiant energy released by varying EM field in the form of Transverse Electromagnetic (TEM) waves. Light wave is EM radiation at very high frequency. The frequency of visible light falls in between IR and UV EM wave. James Clerk Maxwell discovered that he could combine four simple equations, which had been previously discovered, along with a slight modification to describe self-propagating waves of oscillating electric and magnetic fields [38]. The understanding of propagating of light waves using Maxwell's equations in a dielectric medium, is the key to the construction of waveguides. Maxwell's equations relate the electric field  $E$  (V/m), magnetic field  $H$  (A/m), charge density  $\rho$  (C/m<sup>3</sup>), and current density  $J$  (A/cm<sup>2</sup>).

- **Maxwell's first equation (Gauss' Law):** The net electric flux through any closed surface is equal to  $\frac{1}{\epsilon_m}$  times the charge density within that closed surface.

$$\nabla \cdot E = \frac{\rho}{\epsilon_m} \quad (2.1)$$

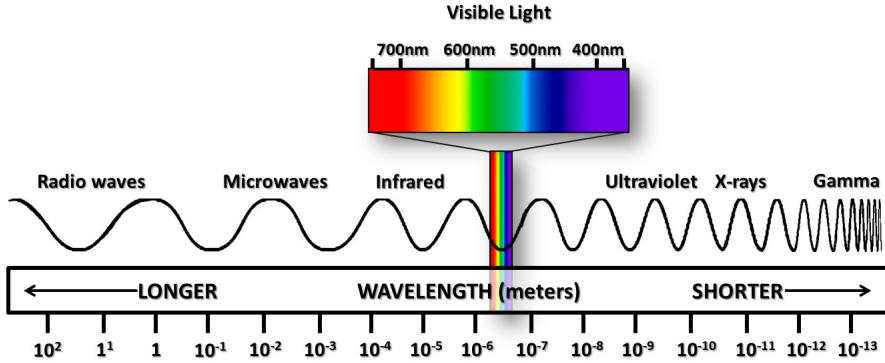


Figure 2.1: The EM wave spectrum

where  $\epsilon_m$  the permittivity of the medium, and del operator,  $\nabla$ , is given by:

$$\nabla = \left( \frac{\partial i}{\partial x}, \frac{\partial j}{\partial y}, \frac{\partial k}{\partial z} \right) \quad (2.2)$$

where  $i$ ,  $j$  and  $k$  are unit vectors in the  $x$ ,  $y$  and  $z$  directions respectively.

- **Maxwell's second equation (Gauss' Law for magnetic field):** The net magnetic flux through a closed surface is always zero since magnetic monopoles do not exist.

$$\nabla \cdot H = 0 \quad (2.3)$$

- **Maxwell's third equation (Faraday's law):** Induced electric field around a closed path is equal to the negative of the time rate of change of magnetic flux enclosed by the path.

$$\nabla \times E = -\mu_m \frac{\partial H}{\partial t} \quad (2.4)$$

where  $\mu_m$  is the magnetic permeability of the medium.

- **Maxwell's fourth equation (Modification of Ampere's law):** The fourth equation states that magnetic fields can be generated in two ways: by electric current (this was the original "Ampere's law") and by changing electric fields (this was "Maxwell's addition") [39].

$$\nabla \times H = J + \epsilon_m \frac{\partial E}{\partial t} \quad (2.5)$$

where  $\epsilon_m$  is the electric permittivity of the medium.

These equations combine into the following wave equation

$$\nabla^2 E - \mu_m \epsilon_m \frac{\partial^2 E}{\partial t^2} = \mu_m \frac{\partial J}{\partial t} + \frac{\nabla \rho}{\epsilon_m}, \quad (2.6)$$

using the curl of curl identity operation given by

$$\nabla^2 E = \nabla(\nabla \cdot E) - \nabla \times (\nabla \times E). \quad (2.7)$$

A general solution to the equation 2.6 in free space, in absence of charge is

$$\vec{E}(z, t) = E_0(x, y) e^{i(\omega t \pm k_0 z)}, \quad (2.8)$$

where  $z$  is direction of propagation of wave in Cartesian coordinates, phase,  $\phi = \omega t \pm k_0 z$  and wave vector propagation constant,  $k_0 = \frac{\partial \phi}{\partial t} = \frac{2\pi}{\lambda}$ , in the direction of propagation of the wave. The propagation constant in medium varies according to  $n_{eff}$ , the effective Refractive index (RI) of the medium and is given by

$$k = n_{eff} k_0, \quad (2.9)$$

where

$$n_{eff} = \sqrt{\epsilon_m \mu_m}. \quad (2.10)$$

Similar calculations for the magnetic field,  $H$  in free space yields,

$$\vec{H}(z, t) = H_0(x, y) e^{i(\omega t \pm k_0 z)} \quad (2.11)$$

In the Fig. 2.2 the electric field and magnetic field propagate in directions perpendicular to each other. Moreover, the direction of propagation is also transverse to the EM field. Hence it is called TEM wave.

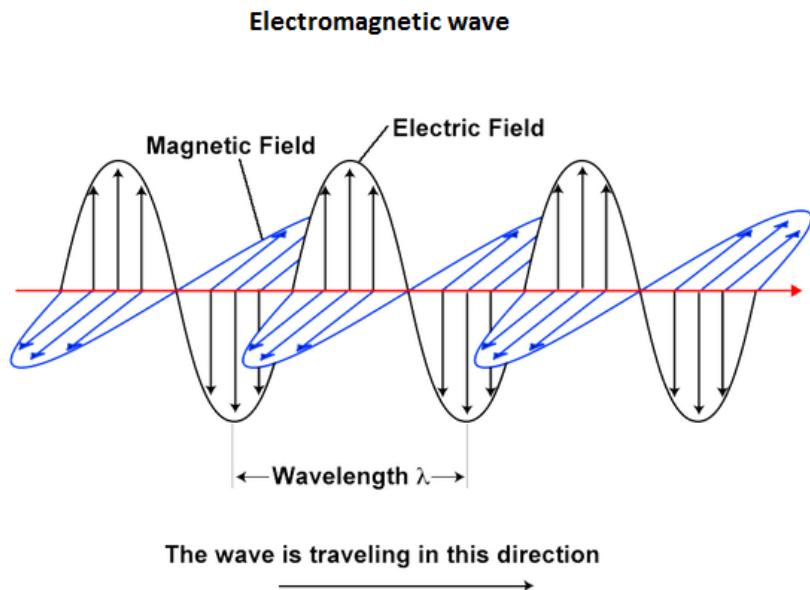


Figure 2.2: Propagation of EM wave

## 2.1.2 Optical waveguides

The waveguide is the essential element of every photonic circuit which can be characterized by the number of dimensions in which light is confined inside it [40]. A planar waveguide confines light in 1-D, which is simple for understanding of the wave propagation using Maxwell's equations. However, for practical applications 2-D confinement is necessary and that is why channel waveguides are used. Structures like photonic crystals even have 3-D confinement properties.

### 2.1.2.1 Planar waveguides

A simple planar waveguide consists of a high-index medium with height  $h$  surrounded by lower-index materials on the top and bottom sides, known as cladding. The RI of the film is  $n_f$ . The RI of the substrate in lower cladding is  $n_s$  whereas, RI of the substrate in upper cladding is  $n_c$ .

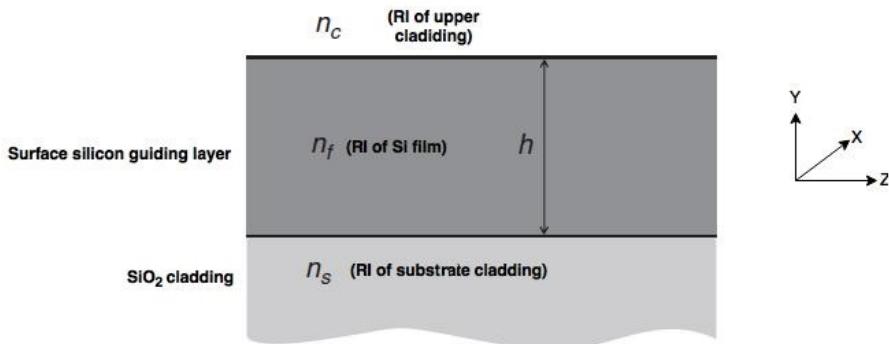


Figure 2.3: A typical planar waveguide where the film is infinite in XZ-plane

For planar waveguides the wave equation for electric field (2.8) and magnetic field (2.11) can be rewritten as follows:

$$\begin{cases} \vec{E}(z, t) = E_x(y)e^{i(\omega t \pm k_0 z)} \\ \vec{H}(z, t) = H_x(y)e^{i(\omega t \pm k_0 z)} \end{cases} \quad (2.12)$$

since in X-direction the film is infinite. After using the homogeneous wave equations for a planar waveguide the following Transverse Electric (TE) and Transverse Magnetic (TM) mode equations can be deduced:

$$\begin{cases} \nabla^2 E_x(y) + (k_0^2 n(y)^2 - k^2) E_x(y) = 0 \\ \nabla^2 H_x(y) + (k_0^2 n(y)^2 - k^2) H_x(y) = 0 \end{cases} \quad (2.13)$$

where  $n(y)$  depends only on a single Cartesian coordinate  $n_{eff} = n(y)$ . These equations can be solved analytically using the various boundary conditions of the waveguides which help in deducing the nature of propagation of the wave in TE and TM mode.

Different kinds of numerical methods like Finite element method (FEM), Finite integration technique (FIT), Finite difference time domain (FDTD), Beam propagation method (BPM) have been developed to decipher the nature of light propagation in waveguides.

### 2.1.2.2 Channel waveguides

As mentioned earlier channel waveguides provide confinement in 2-D which helps in analyzing waveguides in a more practical way. The three main types of channel waveguides are rib, strip and buried waveguides. As depicted in 2.4a, 2.4b, 2.4c the different conceptual structures of the waveguides can be envisaged. While the rib and strip waveguides are designed using etching techniques, the buried waveguide mostly relies on diffusion and epitaxial growth techniques for its fabrication.

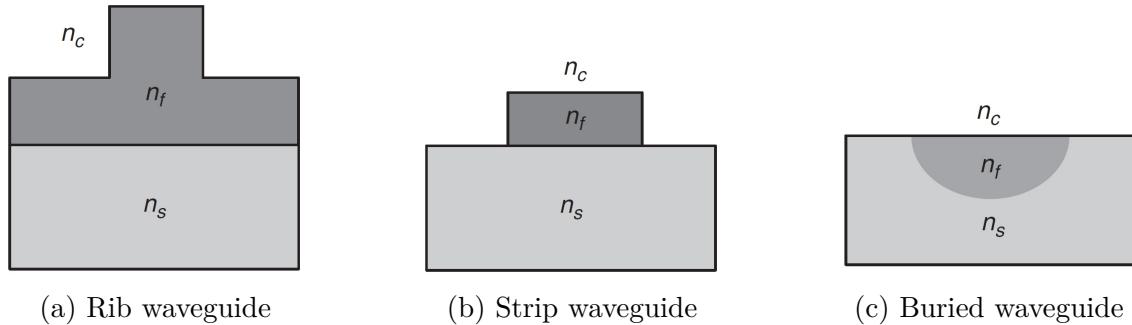


Figure 2.4: Different kinds of design for channel waveguides

- **Design rules of rib waveguides:** While designing these waveguides each of these have specific design rules for optimum performance and low-loss coupling, which has been standardized after years of research [40]. The Single-mode condition (SMC) for *rib waveguides* is as follows:

$$\frac{W}{H} \leq 0.3 + \frac{r}{\sqrt{1 - r^2}}, \quad \text{for } (0.5 \leq r < 1) \quad (2.14)$$

where  $W$ =waveguide width,  $H$ =rib height,  $r$  is ratio of slab height to overall rib height.

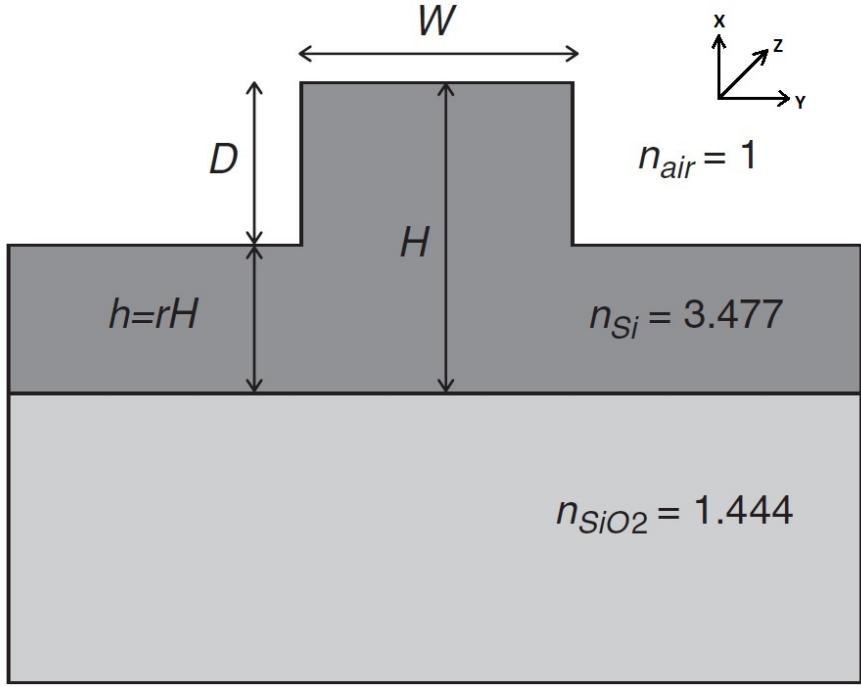


Figure 2.5: Rib waveguide design rules

The main requirements of the waveguide to cater the propagation of waves is that the dimension of the waveguide has to be more than the wavelength of the propagating wave. Depending on the required mode confinement, the width and height are adjusted such that it adheres to 2.5.

- **Design rules of strip waveguides:** In mode confinement of light in optical waveguides the effective mode RI is important. Strip waveguides offer more high RI contrast in comparison to Rib waveguides. This can help in realization of ultra-dense photonic circuits because of high effective mode confinement. This can also achieve small bends which can improve the characterization of different monolithic optical circuits. Sometimes the side walls cannot be etched in a perfectly smooth way causing greater evanescent fields from the waveguides introducing unnecessary coupling and losses. Using simulation for the desired scenario the robust values of the dimensions can be achieved depending on the application.

### 2.1.3 Snell's law and total internal reflection

If light ray propagating in a medium with RI  $n_1$ , impinges on the interface between two media, at an angle  $\theta_1$ , as shown in Figure 2.6, the ray is partially transmitted ( $E_t$ ) and partially reflected ( $E_r$ ). The relationship between the RIs  $n_1$  and  $n_2$ , and the angles of incidence ( $\theta_1$ ) and refraction ( $\theta_2$ ), is given by Snell's law:

$$n_1 \sin \theta_1 = n_2 \sin \theta_2 \quad (2.15)$$

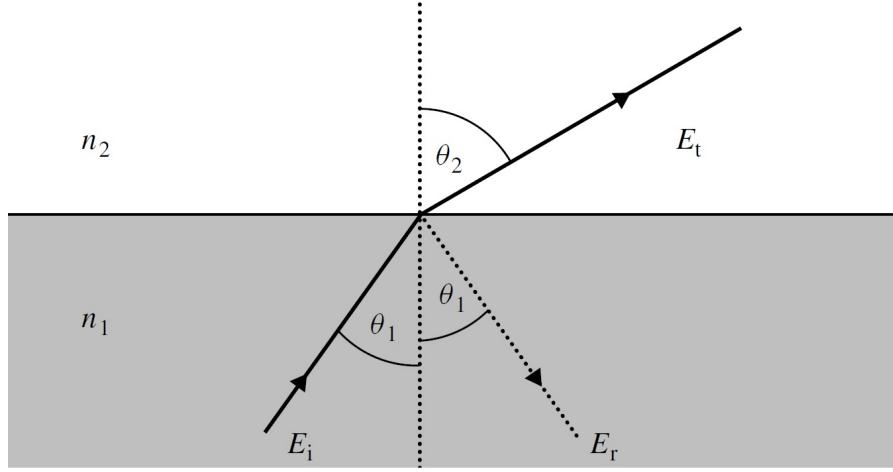


Figure 2.6: Light rays refracted and reflected at the interface of two media

For some angle  $\theta_1$ , the corresponding angle  $\theta_2$  will reach  $90^\circ$ , and hence Snell's law simplifies to:

$$\begin{cases} n_1 \sin \theta_c = n_2 \\ \sin \theta_c = \frac{n_2}{n_1} \end{cases} \quad (2.16)$$

where,  $\theta_c$  is defined as the critical angle. For angles of incidence greater than this critical angle, no light is transmitted and total internal reflection occurs. These properties are important to consider for finding the acceptance angle at which light can be inserted into a waveguide. The ray model helps in understanding of reflection and refraction of light at boundaries between the medium.

#### 2.1.4 Eigenvalue and wave modes

In general, the electric field and magnetic field in the wave equation in 2.8 and 2.11 can be written in its constituent parts in Cartesian coordinates as:

$$\begin{cases} \vec{E} = E_x \hat{x} + E_y \hat{y} + E_z \hat{z} \\ \vec{H} = H_x \hat{x} + H_y \hat{y} + H_z \hat{z} \end{cases} \quad (2.17)$$

The generalized vectorial component of the electric and magnetic field of equation 2.13 for a traveling wave in  $Z$  direction can be combined into the Helmholtz equation as follows:

$$\nabla^2 \Psi(x, y, z) + k_0^2 n^2(x, y) \Psi(x, y, z) = 0 \quad (2.18)$$

where,  $\Psi(x, y, z) = \psi(x, y) e^{-jkz}$  and then the equation 2.18 can be rewritten as,

$$\nabla_{xy}^2 \psi(x, y) + (k_0^2 n^2(x, y) - k^2) \psi(x, y) = 0. \quad (2.19)$$

The equation 2.19 can be solved for  $\psi(x, y)$ , using different numerical analysis methods like FEM, FIT, BPM, FDTD. For optical applications, the main used methods are FEM

(Frequency domain solver), FIT (Time domain solver). The numerical methods first decompose the waveguide into sufficient number small cells (more cells give more robust solution at the cost of increased computing) and then discretization of the refractive index profile is performed. Next the field equations are discretized by replacing the derivatives by their finite difference representations in those cells. In this way a set of linear equations are obtained which can be solved using standard algebraic methods. In general, FIT has a much lower memory footprint.

For given  $\omega$ , the resulting mode problem is an eigenproblem, solved for eigenvectors, i.e., mode profiles  $\psi(x, y)$ , and eigenvalues, from which the corresponding propagation constants  $k$  of the modes are computed. The geometry of the waveguide is given by the transverse dependence of  $\epsilon$ , with effective RI profile, and by appropriately chosen boundary conditions. Each allowed solution is referred to as the *mode of propagation*. For example, when light travels through a rectangular waveguide different modes can be visualized as follows in Fig. 2.7.

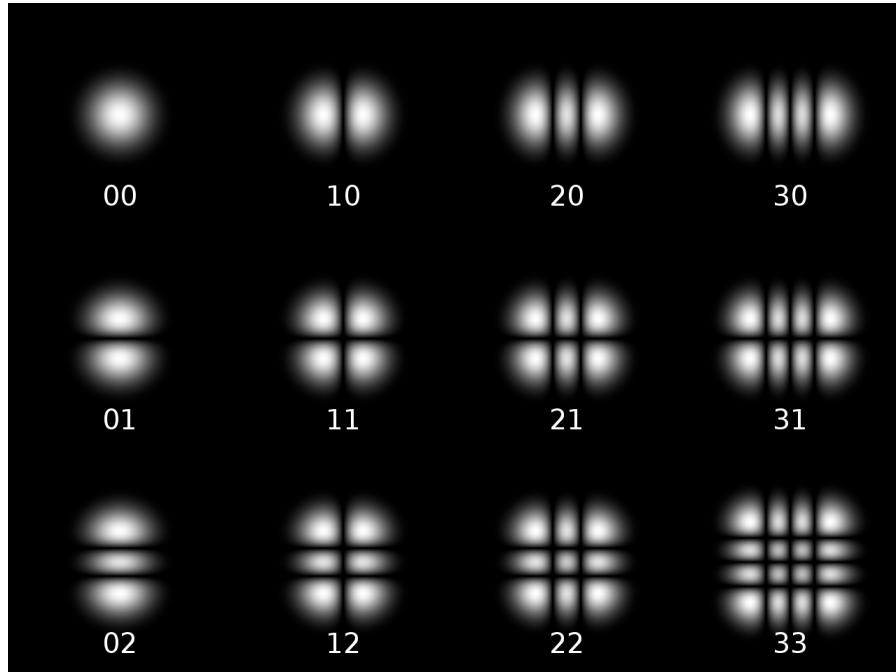


Figure 2.7: Rectangular transverse mode patterns  $TE(mn)$

### 2.1.5 Polarization and transverse modes

In optical waveguides, the transmission distance is limited by several types of dispersion, or spreading of optical pulses as they travel along the waveguide. Dispersion in waveguide is caused by a variety of factors. Intermodal dispersion, caused by the different axial speeds of different transverse modes, limits the performance of multi-mode waveguide. Because single-mode waveguide supports only one transverse mode, intermodal dispersion is eliminated. In single-mode performance is primarily limited by chromatic dispersion (also called group velocity dispersion), which occurs because the RI of silicon varies slightly

depending on the wavelength of the light. PMD, another source of limitation, occurs because although the single-mode waveguide can sustain only one transverse mode, it can carry this mode with two different polarizations, which travel at different propagation velocities. This phenomenon is called birefringence and its effect can be counteracted by polarization-rotator. PMD limits the bandwidth of the waveguide because the spreading optical pulse limits the rate that pulses can follow one another on the waveguide and still be distinguishable at the receiver.

Polarization is the direction of the electric field associated with the propagating wave. In the example in Fig. 2.2 the wave is linearly polarized since the electric field and magnetic field exist in one direction only. In a dielectric optical waveguide, light propagates in linearly polarized modes and the plane in which light is polarized is either vertical or horizontal to the direction of wave, as shown in Fig. 2.8 in single-mode.

#### **2.1.5.1 TE mode**

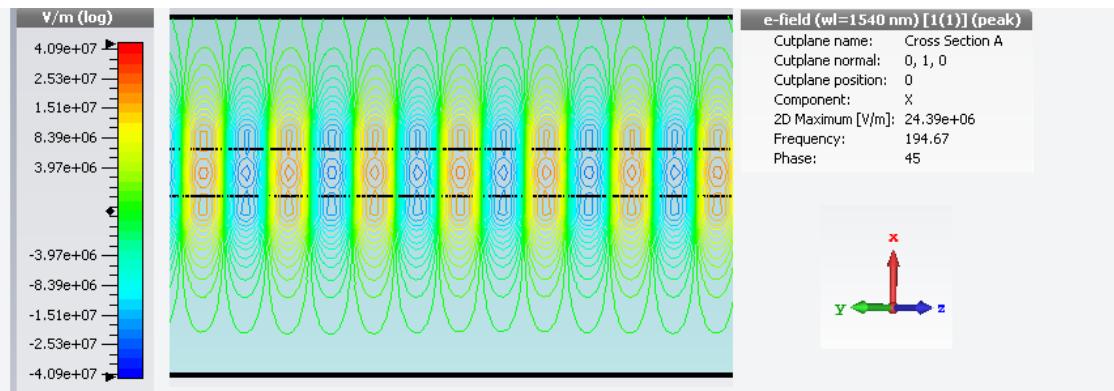
TE mode is the fundamental mode in which there is no electric field in the direction of propagation of light wave. In Fig. 2.8 the electric field lines (blue) are perpendicular to the plane of incidence in TE mode. The plane of incidence is the plane in which optical waves strike the surface of the waveguide.

#### **2.1.5.2 TM mode**

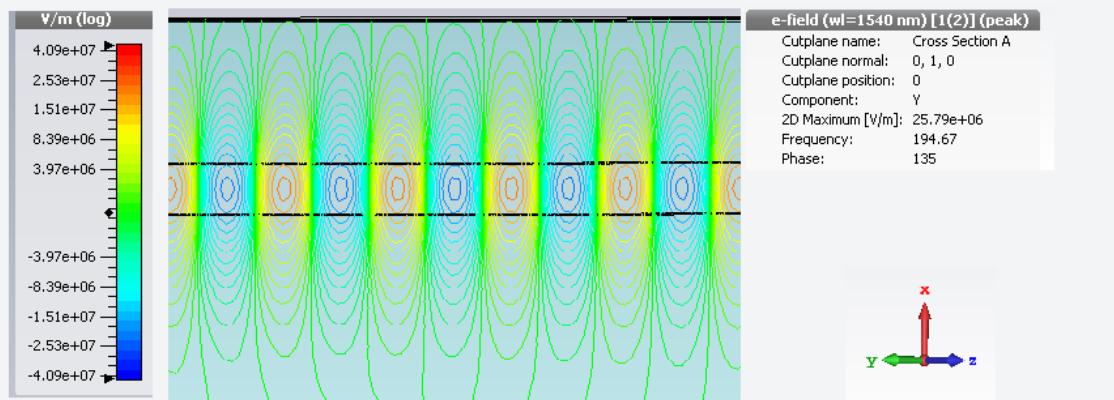
TM mode is the fundamental mode in which there is no magnetic field in the direction of propagation of light. In Fig. 2.8 it can be seen that magnetic field (red lines) are perpendicular to the plane of incidence in TM mode.

#### **2.1.5.3 Quasi-TE and Quasi-TM mode**

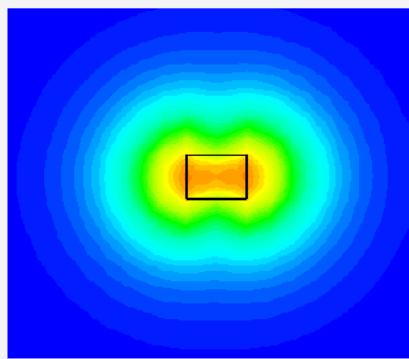
Practically, waveguide cores have electric and magnetic fields that slice through air and the cladding substrate. Hence they do not support pure TE and TM modes. However, since most the power is contained under the waveguide core and inside just the cladding, TE and TM modes can be a good approximation. Generally, in these modes there is some field component in the direction of propagation as well. This is known as quasi-TE and quasi-TM mode.



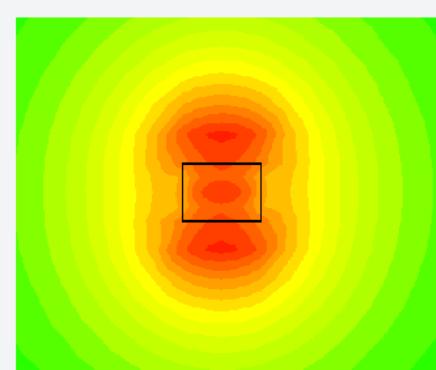
TE fundamental mode viewed from top on Y-cutplane



TM fundamental mode viewed from top on Y-cutplane



TE fundamental mode viewed on Z-cutplane



TM fundamental mode viewed on Z-cutplane

Figure 2.8: TE and TM fundamental mode in a waveguide using CST simulation

## 2.1.6 Confinement factor

Often it is necessary to know the confined power inside the core of the waveguide which helps in figuring out the waveguide mode. The confinement is also a measure of the proportion of the power in a given mode that lies within the core [40].

$$\text{Confinement factor} = \frac{\int_{-H/2}^{H/2} E_x^2(y) dy}{\int_{-\infty}^{\infty} E_x^2(y) dy} \quad (2.20)$$

Confinement factor is an important measure which is function of various factors like polarization, RI difference between the core and cladding, mode number etc.

## 2.1.7 Jones calculus

Polarized light can be represented using Jones calculus. Polarized light is represented using *Jones vector* and linear optical elements are represented by *Jones matrices*. When light crosses an optical element the resulting polarization of the emerging light is found by taking the product of the Jones matrix of the optical element and the Jones vector of the incident light. *Jones calculus* is only applicable to light that is already fully polarized [41].

### 2.1.7.1 Jones vector

The Jones vector describes the SOP of light in free space or another homogeneous isotropic non-attenuating medium, where the light can be properly described as transverse waves [41]. The Jones vector is a complex vector that is a mathematical representation of a real wave. A typical representation of the electric field for the optical wave described in 2.8 can be as follows:

$$E = \begin{pmatrix} E_x(t) \\ E_y(t) \\ 0 \end{pmatrix} = \begin{pmatrix} E_x e^{i(\omega t - kz + \phi_x)} \\ E_y e^{i(\omega t - kz + \phi_y)} \\ 0 \end{pmatrix} = \begin{pmatrix} E_x e^{i\phi_x} \\ E_y e^{i\phi_y} \\ 0 \end{pmatrix} e^{i(\omega t - kz)} \quad (2.21)$$

where  $\phi_x$  and  $\phi_y$  indicate the phasor notation. The Jones vector of the plane wave is described by:

$$\begin{pmatrix} E_x e^{i\phi_x} \\ E_y e^{i\phi_y} \end{pmatrix} \quad (2.22)$$

and the intensity of the optical,  $I$  wave can be written as,

$$I = |E_x|^2 + |E_y|^2 \quad (2.23)$$

Generally, when considering Jones vector a wave of unit intensity is required for the consideration polarization, so Jones vector is noted using an unit vector where,

$$\bar{E}\bar{E} = 1 \quad (2.24)$$

where  $\bar{E}$  is the complex conjugate of  $E$ . In general the Jones representation of a normalized elliptically polarized beam with azimuth  $\theta$  and elliptical angle  $\epsilon$  is given by,

$$e^{i\phi} \begin{pmatrix} \cos \theta \cos \epsilon - j \sin \theta \sin \epsilon \\ \sin \theta \cos \epsilon - j \cos \theta \sin \epsilon \end{pmatrix} \quad (2.25)$$

where  $e^{i\phi}$  is an arbitrary phase vector and  $\phi = \phi_x - \phi_y$ . So, for example a linear polarization of TE mode can be represented as,

$$\begin{pmatrix} 1 \\ 0 \end{pmatrix} \quad (2.26)$$

since,  $\theta = 0$  and  $\epsilon = 0$ .

### 2.1.7.2 Jones matrix

Jones matrix is the formal representation of the various optical elements such as lenses, beam splitters, mirrors, phase retarders, polarizers at arbitrary angles that can modify polarization. They generally operate on Jones vector and helps in comprehend situations which light encounters multiple polarization elements in sequence. In these situations the products of the Jones matrices can be used to represent the transfer matrix. This situation can be represented using,

$$[E_{output}] = J_{system}[E_{input}] \quad (2.27)$$

where  $E_{input}$  is the input field into the optical system and  $E_{output}$  is the generated output field represented using Jones vector. The matrix  $J_{system}$  is the Jones matrix of the optical system comprising of a series of polarization devices. If there are  $N$  devices in the system then the final transfer matrix comes out as,

$$J_{system} = J_N J_{N-1} \dots J_2 J_1 \quad (2.28)$$

where  $J_N$  is the Jones matrix for  $n^{th}$  polarizing optical element.

### 2.1.7.3 Jones matrix for polarizing optical systems

To construct optical waveguides for polarization rotation it is imperative to deal with the basic principles of standard available optical systems. Here, the fundamental principles of polarizer and wave plates are interpreted using Jones calculus.

#### Polarizer

Polarizers have an index of refraction which depends on orientation electric field propagation. If any optical system has a transmission axis and an absorption axis for electric fields, then lights will be passed along he transmission axis and absorbed along the other axis. So, the Jones matrix of a polarizer making an angle  $\theta$  with the X-axis will come out as,

$$\begin{pmatrix} \cos^2 \theta & \sin \theta \cos \theta \\ \sin \theta \cos \theta & \sin^2 \theta \end{pmatrix} \quad (2.29)$$

## Wave plates

Wave plates are phase retarders which are made of birefringent crystals. Wave plates can be conceptualized as two polarizers kept apart at certain distance  $d$ , such that their polarization axes are apart orthogonally ( $90^\circ$ ). The phase difference as light passes through this setup of thickness  $d$  is [42],

$$(k_{slow} - k_{fast}) d = \frac{2\pi d}{\lambda_{vac}} (n_{slow} - n_{fast}) \quad (2.30)$$

In, general the Jones matrix for a wave plate is given by [42],

$$\begin{pmatrix} \cos^2 \theta + \xi \sin^2 \theta & \sin \theta \cos \theta - \xi \sin \theta \cos \theta \\ \sin \theta \cos \theta - \xi \sin \theta \cos \theta & \sin^2 \theta + \xi \cos^2 \theta \end{pmatrix} \quad (2.31)$$

where  $\xi$  is calculated based on the type of wave plate. The following equations addresses some general scenarios:

$$\begin{cases} \xi = e^{i\pi/2}, & \text{where, } (k_{slow} - k_{fast}) d = \pi/2 + 2\pi m, \text{ for quarter-wave plate} \\ \xi = e^{i\pi}, & \text{where, } (k_{slow} - k_{fast}) d = \pi + 2\pi m, \text{ for half-wave plate} \end{cases} \quad (2.32)$$

and  $m \in \mathbb{Z}$ .  $\xi$  is the phase delay of the wave plates. Similar concept is used in the construction of PR waveguides which will be discussed in later sections shortly.

### 2.1.8 Poincaré sphere and state of polarization

To view a complete representation of all the polarization ellipses generated using Jones vectors, a spherical structure with unit radius is used, which is known as Poincaré sphere. If the orientation in space of the ellipse of polarization is determined by the azimuth,  $\theta$  and ellipticity,  $\epsilon$  then that point can be completely characterized by its longitude  $2\theta$  and latitude  $2\epsilon$ . The north and south poles represent the right-handed and left-handed circular polarization respectively. In general the diametrically opposite points represent pairs of orthogonal polarization. The SOP and its corresponding location in the Poincaré sphere is visualized in the Fig. 2.9. To go from one SOP to another the polarized light can be passed through various optical components which can be computed using the Jones matrix and the corresponding SOP can be depicted on the Poincaré sphere as well.

The SOP of any wave are figures of merit (FOM) for PR and are described using **Polarization extinction ratio (PER)** and polarization phase,  $\phi$  given by the following equations:

$$\begin{cases} PER_{TE-TM} = 10 \log \frac{P_{TM}}{P_{TE}} \\ PER_{TM-TE} = 10 \log \frac{P_{TE}}{P_{TM}} \\ \phi = \phi_x - \phi_y \end{cases} \quad (2.33)$$

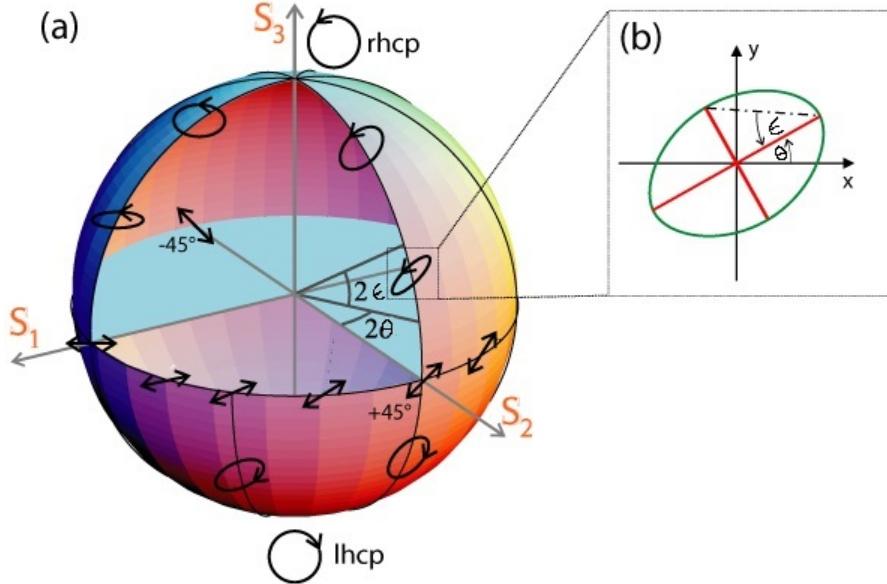


Figure 2.9: (a) Representation of the Poincaré sphere (b) Representation of the ellipse parameters [43]

For complete polarized light, the point on the Poincaré sphere must be fixed on time which requires,

$$\frac{E_x(t)}{E_y(t)} = \text{constant} \quad (2.34)$$

and,

$$\phi = \phi_x(t) - \phi_y(t) = \text{constant} \quad (2.35)$$

Apart from the afore mentioned FOM, another important characteristic which must be optimized is **Insertion loss**. It is the loss of signal power resulting from the insertion of a device in a transmission line or optical fiber and is usually expressed in decibels (dB). If the power transmitted to the load before insertion is  $P_{in}$  and the power received by the load after insertion is  $P_{out}$ , then the Insertion loss (IL) in dB is given by,

$$IL(\text{dB}) = 10 \log_{10} \frac{P_{in}}{P_{out}} \quad (2.36)$$

## 2.1.9 Stoke's parameter

Quasi-monochromatic waves are mathematically treated using Stokes parameters ( $S_0, S_1, S_2, S_3$ ), which constitute a vector generally known as Stokes vectors. Stokes vectors are used to keep track of the partial polarization (and attenuation) of a light beam in terms of total intensity (I), degree of polarization (p) and ellipse parameters, as the light progresses

through an optical system. A Stokes vector can generally be represented as,

$$\vec{S} = \begin{pmatrix} S_0 \\ S_1 \\ S_2 \\ S_3 \end{pmatrix} \quad (2.37)$$

where,

$$\begin{cases} S_0 = I \\ S_1 = I_p \cos 2\theta \cos 2\epsilon \\ S_2 = I_p \sin 2\theta \cos 2\epsilon \\ S_3 = I_p \sin 2\epsilon \end{cases} \quad (2.38)$$

Here,  $I_p, 2\theta, 2\epsilon$  are the spherical coordinates of the 3-D vector of Cartesian coordinates  $(S_1, S_2, S_3)$ . So, given the Stokes parameters, the spherical coordinates  $(p, 2\theta, 2\epsilon)$  can be obtained and represented by a point inside the Poincaré sphere using the following:

$$\begin{cases} I = S_0 \\ p = \sqrt{S_1^2 + S_2^2 + S_3^2} \\ 2\theta = \tan^{-1} \frac{S_0}{S_1} \\ 2\epsilon = \tan^{-1} \frac{S_3}{\sqrt{S_1^2 + S_2^2}} \end{cases} \quad (2.39)$$

The prescribed notations are portrayed on the Poincaré sphere in the following Fig. 2.10.

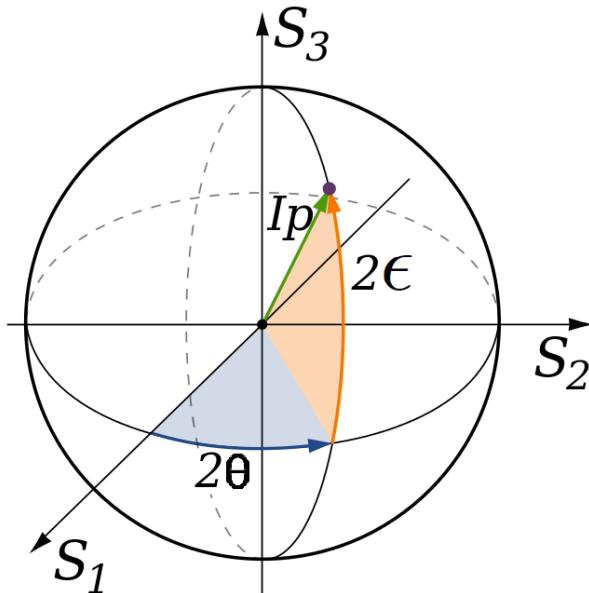


Figure 2.10: Poincaré sphere, on or beneath which the three Stokes parameters  $[S_1, S_2, S_3]$  are plotted in Cartesian coordinates [44]

### 2.1.10 Coupled mode theory

In a waveguide, an ideal mode is an eigenvector of a propagation constant. Mode coupling enables transfer of energy from one ideal mode to another, during propagation. Mode coupling can be induced by introducing randomness in the waveguide. This can be achieved through random or intentional index perturbations, bends and stresses within a waveguide, or by introducing another independent waveguide structure in close proximity (coupled waveguides in close proximity are modeled as a single structure, forming supermodes). The pairwise coupling strength between two modes depends on a dimensionless ratio between the coupling coefficient (per unit length) and the difference between the two modal propagation constants. Hence, a given perturbation may strongly couple modes having nearly equal propagation constants, but weakly couple modes having highly unequal propagation constants. PMD and PDL have long been described by field coupling models, in which phase dependent coupling of modal fields is described by complex coefficients. Field coupling models describe not only a redistribution of energy among modes, but also how eigenvectors and their eigenvalues depend on the mode coupling coefficients [45].

**Perturbation Analysis:** Supermodes can be represented as weighted sum of individual guided modes. If two modes are represented by  $\psi_1(x, y)$  and  $\psi_2(x, y)$  in the different waveguides along with the coupling between two modes as  $X_i(z)$ , then the supermode can be written using Helmholtz identity as,

$$\Psi(x, y, z) = X_1(z)\psi_1(x, y) + X_2(z)\psi_2(x, y) \quad (2.40)$$

The uncoupled modes,  $\psi_1$  and  $\psi_2$  satisfy the following propagation equations with propagation constants  $k_1$  and  $k_2$ ,

$$\begin{cases} \frac{dX_1}{dz} = -jk_1X_1 \\ \frac{dX_2}{dz} = -jk_2X_2 \end{cases} \quad (2.41)$$

A known solution for 2.41 is:

$$\begin{cases} X_1(z) = e^{-jk_1z} \\ X_2(z) = e^{-jk_2z} \end{cases} \quad (2.42)$$

Coupled mode theory postulates that to describe a perturbed system the linear coupling terms need to be added as,

$$\begin{cases} \frac{dX_1}{dz} = -jk_1X_1(z) - j(\kappa_{11}X_1 + \kappa_{12}X_2) \\ \frac{dX_2}{dz} = -jk_2X_2(z) - j(\kappa_{21}X_1 + \kappa_{22}X_2) \end{cases} \quad (2.43)$$

where,  $\kappa_{ij}$ ,  $\forall (i, j) \in [1, 2]$  are the linear coefficients which can be understood using the scattering matrix as,

$$\begin{pmatrix} \kappa_{11} & \kappa_{12} \\ \kappa_{21} & \kappa_{22} \end{pmatrix} \quad (2.44)$$

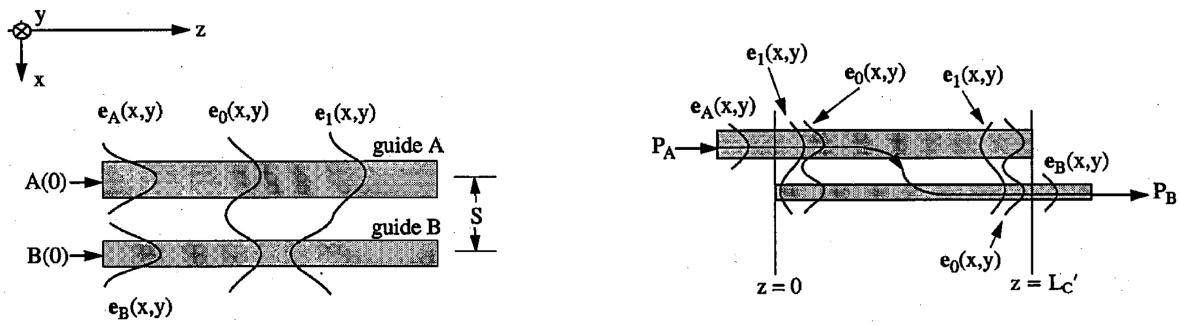
where,

$$\left\{ \begin{array}{l} \kappa_{11} = \frac{1}{2} k_0^2 \int \int (n_{12}^2 - n_1^2) \psi_1^2 dx dy \\ \kappa_{12} = \frac{1}{2} k_0^2 \int \int (n_{12}^2 - n_1^2) \psi_1 \psi_2 dx dy \\ \kappa_{21} = \frac{1}{2} k_0^2 \int \int (n_{12}^2 - n_2^2) \psi_1 \psi_2 dx dy \\ \kappa_{22} = \frac{1}{2} k_0^2 \int \int (n_{12}^2 - n_2^2) \psi_2^2 dx dy \end{array} \right. \quad (2.45)$$

Here,  $\kappa_{11}$  and  $\kappa_{22}$  are the reflection coefficients and  $\kappa_{12}$  and  $\kappa_{21}$  are the coupling coefficients. Normally, it is assumed that the modes are normalized, and propagate in a lossless system with symmetric coupling coefficients. Hence,

$$\kappa_{12} = \kappa_{21} \quad (2.46)$$

Coupling coefficients and phase mismatch are important factors for power exchange between different modes. In 2.11a both the waveguides are excited where as in 2.11b only waveguide  $B$  is excited.



(a) Individual and normal modes in two different waveguides

(b) Power transfer from arm  $A$  to arm  $B$  by normal-mode coupling

Figure 2.11: Description of the directional coupler under coupled-mode and normal-mode

In 2.11b for no phase mismatch complete power exchange occurs. This is why phase matching is an important criteria for mode coupling. The coupling length,  $L_c = \pi/2\kappa$ .

Coupling mode theory has been successfully applied to the modeling and analysis of various guided-wave optoelectronic devices, such as optical directional couplers made of thin film and channel waveguides, multiple waveguide lenses, phase-locked laser arrays, distributed feedback lasers and distributed Bragg reflectors, grating waveguides and couplers, nonparallel and tapered waveguide structures, Y-branch waveguides, TE/TM polarization converters, mode conversion and radiation loss in slab waveguides, residual coupling among scalar modes. It has also been used to study the wave coupling phenomena in nonlinear media such as harmonic generation in bulk and guided-wave devices, and nonlinear coherent couplers [46].

## 2.2 Polarization rotator (PR)

For an overall robust network, PRs are necessary in optical fiber and OEIC, which are realized in different approach.

### 2.2.1 Optical fiber PR

In an ordinary (non-polarization-maintaining) fiber, TE and TM have the same nominal phase velocity due to the fiber's circular symmetry. However tiny amounts of random birefringence in such a fiber, or bending in the fiber, will cause a tiny amount of crosstalk from the TM to TE mode. And since even a short portion of fiber, over which a tiny coupling coefficient may apply, is many thousands of wavelengths long, even that small coupling between the two polarization modes, applied coherently, can lead to a large power transfer to the TE mode, completely changing the wave's net state of polarization. Since that coupling coefficient was unintended and a result of arbitrary stress or bending applied to fiber, the output state of polarization will itself be random, and will vary as those stresses or bends vary; it will also vary with wavelength.

Polarization-maintaining fibers work by intentionally introducing a systematic linear birefringence in the fiber, so that there are two well defined polarization modes which propagate along the fiber with very distinct phase velocities. The beat length  $L_b$  of such a fiber (for a particular wavelength) is the distance (typically a few millimeters) over which the wave in one mode will experience an additional delay of one wavelength compared to the other polarization mode. Thus a length  $\frac{L_b}{2}$  of such fiber is equivalent to a half-wave plate. Now consider that there might be a random coupling between the two polarization states over a significant length of such fiber. At point 0 along the fiber, the wave in polarization mode 1 induces an amplitude into mode 2 at some phase. However at point  $\frac{L_b}{2}$  along the fiber, the same coupling coefficient between the polarization modes induces an amplitude into mode 2 which is now 180° out of phase with the wave coupled at point zero, leading to cancellation. At point  $L_b$  along the fiber the coupling is again in the original phase, but at  $\frac{3L_b}{2}$  it is again out of phase and so on. The possibility of coherent addition of wave amplitudes through crosstalk over distances much larger than  $L_b$  is thus eliminated. Most of the wave's power remains in the original polarization mode, and exits the fiber in that mode's polarization as it is oriented at the fiber end [47].

Electrically driven polarization controller currently available provides a simple, efficient means to manipulate the state of polarization within a singlemode fiber. These operate with negligible insertion and return losses at 100Hz response speed with continuous polarization control capability at low voltage [48].

## 2.2.2 On-chip PR

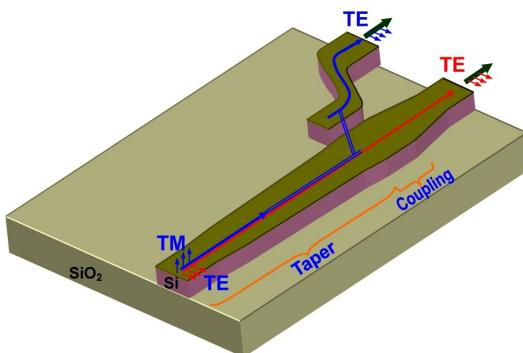
The currently available OEIC PRs can be classified under two categories as passive and active PR. In the passive PRs the waveguide structures are designed in a specific way to manipulate the effective RI of the waveguide, in order to obtain the desired polarization. The RI cannot be manipulated or tuned once fabricated. Whereas, in active PRs, the effective RI can be manipulated by thermo-optic or quantum effects.

### 2.2.2.1 Passive PR

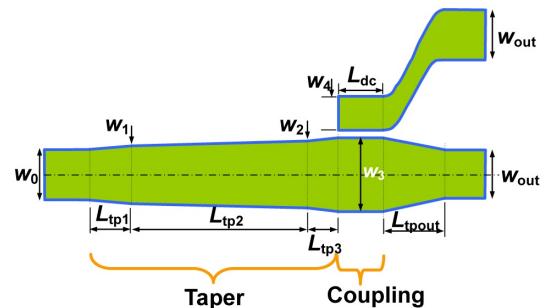
The fields in TE and TM mode are orthogonal (i.e. no coupling exists) and are of different geometry. Thus asymmetric structure in both horizontal and vertical directions are required to break the symmetry, which is accomplished by using different principles viz. mode coupling [32, 49, 31], mode evolution [50, 34, 51, 52, 53] and mode hybridization [54, 30, 55, 29], described in the following sections. All these principles are based on the coupling mode theory described in 2.1.10.

**Mode coupling:** Mode coupling PR includes a pair of waveguides running parallel to each other, with coupled evanescent fields within close proximity. When two modes with orthogonal polarizations have equal effective RIs, strong mode coupling occurs in between the waveguides (generally asymmetric directional couplers), and with proper taper orientation and design, length of coupling region, one mode can be effectively converted to the other.

- Design: Ultra-compact polarization splitter-rotator based on silicon nanowires



(a) Schematic of the PR



(b) Structure of the PR

Figure 2.12: PR using mode coupling, by Dai and Bowers [32]

The coupler (Fig. 2.12a) consists of 2 waveguides parallel to each other. The section where coupling occurs is shown in Fig. 2.12b. The taper structure is singlemode at the input end ( $W_0$ ) while it becomes multimode at the other end ( $W_3$ ). When light propagates along the taper structure, the TM fundamental mode launched at the narrow end ( $W_0$ ) is converted to the first higher-order TE mode at the wide end

$(w_3)$  because of the mode coupling between them. Another narrow optical waveguide ( $W_4$ ) is then placed close to the wide waveguide ( $W_3$ ) and an asymmetrical directional coupler is formed. By using this asymmetrical directional coupler, the first higher-order TE mode in the wide waveguide is then coupled to the TE fundamental mode of the adjacent narrow waveguide. In this way, the input TM fundamental mode at the input waveguide is finally converted into the TE fundamental mode at the cross port of asymmetrical directional coupler. On the other hand, the input TE polarization keeps the same polarization state when it goes through the adiabatic taper structure. In the region of the asymmetrical directional coupler, the TE fundamental mode in the wide waveguide could not be coupled to the adjacent narrow waveguide because of the phase mismatching. In this way, TE- and TM- polarized light are separated while the TM fundamental mode is also converted into TE fundamental mode [32].

Various other designs for mode coupling have also been proposed [31, 49], which work on the same principle.

- **Problem of mode coupling:** The main problem of mode coupling is that directional couplers are not very broadband. Moreover, due to the large birefringence of silicon waveguides, the conversion usually occurs between fundamental TM and high order TE modes and subsequently the high order TE mode is converted to the fundamental TE mode.

**Mode evolution:** The mode evolution based PR includes a single waveguide core. The waveguide is designed in such a way that the cross-section of the waveguide varies along the direction of propagation, both in width and height. This changes polarization from TE to TM or vice versa gradually in propagation direction, under adiabatic transition conditions. Since, the cross-section changes gradually and not abruptly, the PER is high in these type of PRs.

□ Design A: Mode evolution PR based on single taper

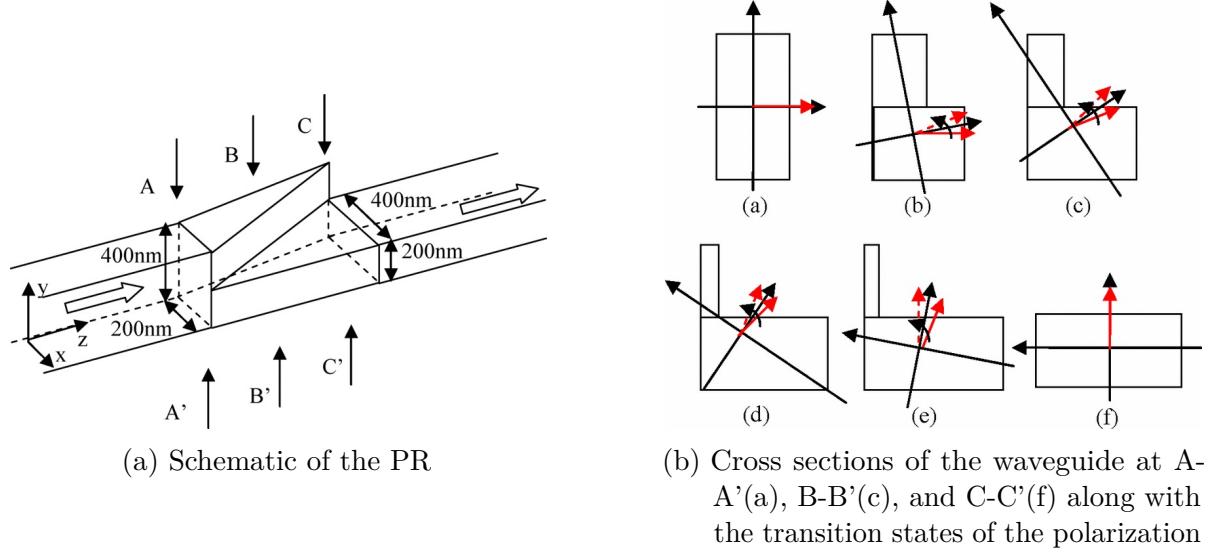


Figure 2.13: PR using mode evolution, by Zhang *et al.* [50]

The PR (Fig. 2.13a) consists of the variable cross section for polarization rotation. The transition region of the rotator was divided into N sections. Each section was considered as a uniform asymmetrical waveguide like the rotator in [56]. The length of each section was its half-beat length. The half-beat length of the  $n^{th}$  section is  $L_\pi^n = (\pi / (\beta_1^n - \beta_2^n))$ , where  $\beta^n = (2\pi/\lambda) n_{eff}^n$  and  $\beta_1^n$  and  $\beta_2^n$  are the propagation constants of the two fundamental modes in the  $n^{th}$  section. After propagating in the  $n^{th}$  section, the polarization will rotate  $2\Delta\varphi_n$  toward the optical axis, where  $\varphi_n$  is the angle between the optical axis and the polarization of the incident light. The overall rotator should satisfy  $\sum_n 2\Delta\varphi_n = 90^\circ$ , to achieve a rotation of  $90^\circ$  in the cascaded sections. Fig. 2.13b shows the rotation procedure [50].

□ Design B: Mode evolution PR composed of an asymmetric-rib waveguide and a tapered waveguide

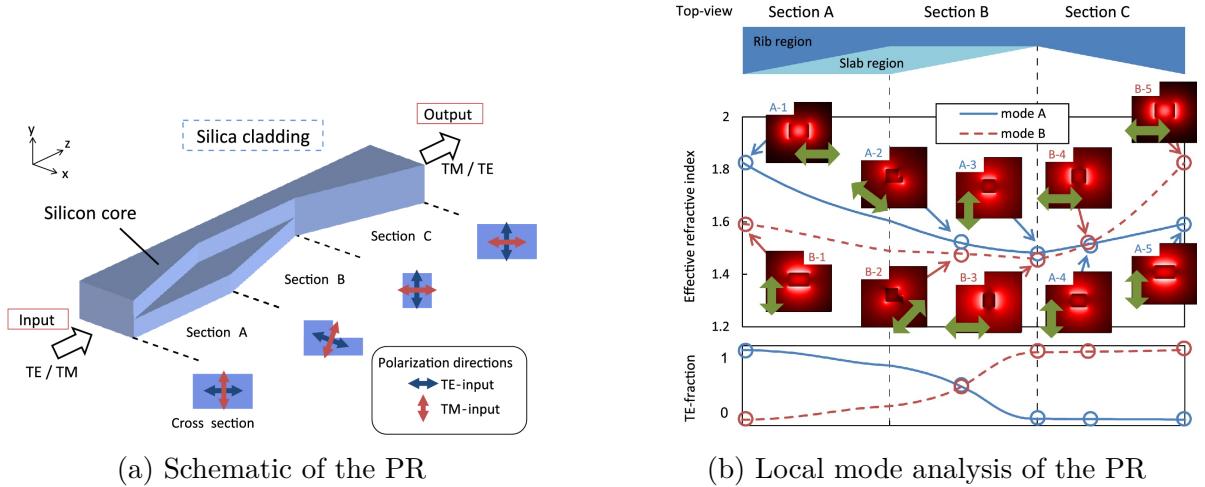


Figure 2.14: PR using mode evolution, by Goi *et al.* [53]

The PR (Fig. 2.14a) consists of the polarization rotation sections(A and B) with an asymmetric rib waveguide and the mode size conversion section(C) with a nano-tapered waveguide. This design provides both vertical and horizontal asymmetry.

Apart from these, other designs for mode evolution have also been proposed [34, 51, 52], which has the same basic principle.

□ **Problem of mode evolution:** In mode evolution, silicon waveguide is specially designed with tapers to enable gradual mode conversion between orthogonal polarization states. This kind of design increases the complexity of fabrication. Also, sharp tips at the end of tapers necessary for low conversion loss are also difficult to make. A pure silicon solution is proposed in [50], but in their structure the input and output silicon waveguides have different thicknesses. The structure in [53] solves this problem at the cost of a longer device length of 230 $\mu\text{m}$ . Efficient design of these kind of PRs require trade-off between scattering losses at the tapers versus the device length.

**Mode hybridization:** Mode hybridization works by abruptly breaking the symmetry of the silicon waveguide cross section. The propagation modes are hybridized due to introduced asymmetry, allowing optical power to be transferred periodically between the two desired polarization states. The propagation modes excite simultaneously the two fundamental hybrid modes of the asymmetric waveguide, which evolve with different propagation constant. The rotation of 90° is achieved through interference of the two hybridized modes for a length of  $L_\pi$ , according to the principle of wave plates described mathematically, using 2.32.

□ **Design A: Asymmetric silicon nanowire waveguide as compact PR**

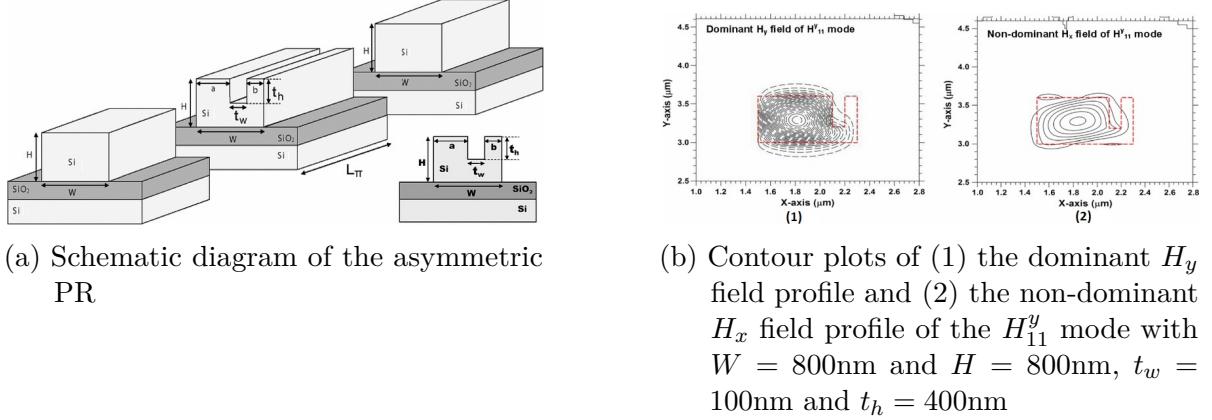
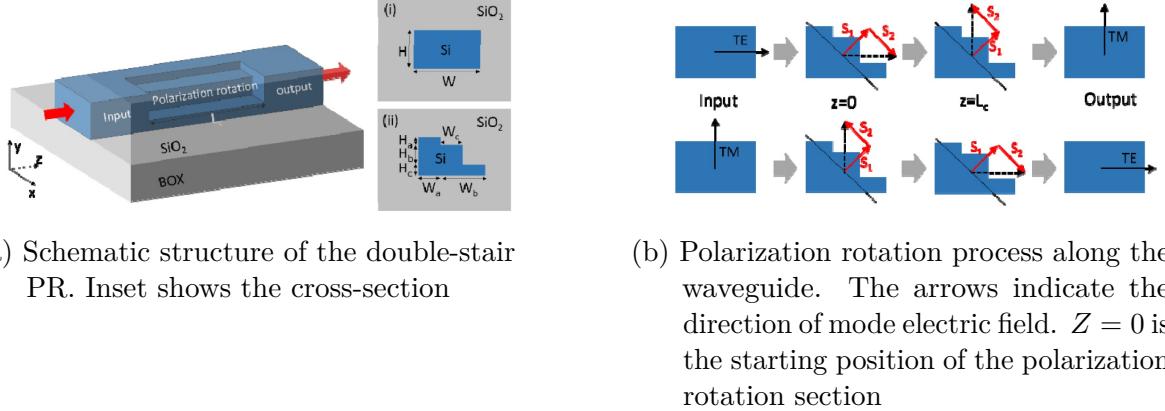


Figure 2.15: PR using mode hybridization, by Leung *et al.* [30]

Fig. 2.15a depicts the single-stage polarization rotator, which consists of two Si strip waveguides with straight sidewalls, where both are butt coupled to an Si asymmetric strip polarization rotator waveguide in the middle. In the design of a polarization rotator, an asymmetric section which supports the highly hybrid modes is sandwiched between two standard Si waveguides. When a quasi-TE (or quasi-TM) mode from a standard Si waveguide with its polarization angle at nearly zero degrees (or  $90^\circ$ ) is launched into the asymmetric section (which supports highly hybrid modes with polarization direction  $\pm 45^\circ$ ), then both of them are excited almost equally to satisfy the continuity of the  $E_t$  and  $H_t$  fields at that interface. These two highly hybrid modes travel along the asymmetric sections. The half-beat length is a key parameter used in order to identify the optimum length of this asymmetrical section to achieve the maximum polarization rotation. The half-beat length is defined as  $L_\pi = \pi/\Delta\beta$ , where  $\Delta\beta$  is the difference between the propagation constants of the two hybrid modes. After propagating a distance  $L = L_\pi$ , the original phase condition between the highly polarized modes would be reversed, and the polarization state of the superimposed modes would be rotated by  $90^\circ$ . If a standard Si waveguide (with smaller modal hybridness) is placed at this position, this quasi-TM (or quasi-TE) mode would propagate without any further polarization rotation [30].

□ **Design B: Efficient silicon PR based on mode-hybridization in a double-stair waveguide**

Due to the sudden abruptness introduced in the previous design (Design A) of mode hybridization, the PER was low. Hence, the abruptness is introduced more gradually in the design, as shown in Fig. 2.16b. The design looks like two successive stairs and hence it is called double-stair waveguide. The PR [28], based on a double-stair silicon waveguide fabricated with three etch steps as described in Fig.2.16a is better compared to the two-etch-step structure with single-stair cross section [57] because of the higher PER and broader optical bandwidth achieved.



(a) Schematic structure of the double-stair PR. Inset shows the cross-section  
(b) Polarization rotation process along the waveguide. The arrows indicate the direction of mode electric field.  $Z = 0$  is the starting position of the polarization rotation section

Figure 2.16: PR using double-stair waveguide mode hybridization, by Xie *et al.* [28]

The schematics of the PR (Fig. 2.16a) consists of the polarization rotation sections and describes the mode conversion along the waveguide.

Other designs for mode hybridization have also been proposed [54, 55], which work on the same principle.

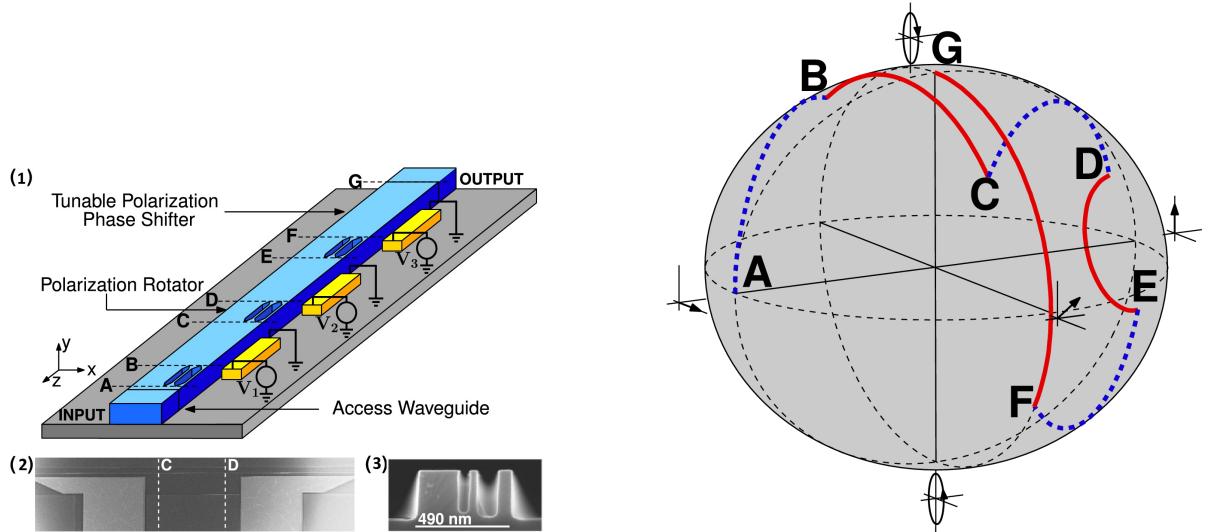
- **Problem of mode hybridization:** The narrow trenches ( $\sim 10$  nm wide) required for mode hybridization are difficult to pattern and etch with controllable profiles. Recently, a PR [57] is realized on a simple strip waveguide by cutting one upper corner of the waveguide in a two-step etch process following the original idea in [56]. The pure silicon solution [57], without the need of extra materials is attractive, but the measured PER is relatively low around  $\sim 6$  dB within a  $\sim 30$  nm bandwidth. Although, the double-stair waveguide [28], offers good results but they exhibit wavelength-dependent loss because its working principle relies on interference.

### 2.2.2.2 Active PR

An active PR is generally achieved by multiple tunable controllers which gives a good trade-off between integration and performance.

**Tunable PR with thermo-optic effect:** The PRs mainly change the PER, whereas the Tunable polarization phase shifters (TPPS) control the polarization phase. The TPPS are implemented using waveguide heaters placed alongside the waveguide to avoid losses due to interaction of the evanescent field with the metal. The intensity of the waveguide heaters are electrically controlled.

□ Design: Tunable PR with phase shifters



(a) Schematic of the polarization controller along with the cross section of the PR, which uses mode hybridization. The cross section of mode hybridization PR can be seen in (3)

(b) Evolution of SOP throughout the device

Figure 2.17: PR control using three PR and three TPPS, by Merenguel *et al.* [35]

In the passive PRs, the individual PR had to produce an exact polarization conversion. This was overcome by the design of the PR in Fig. 2.17a. The PR (Fig. 2.17a) consists of three PRs and three TPPS which control the SOP. The operation of the device is illustrated in Fig. 2.17b using the Poincaré sphere 2.1.8. First, a certain PR will be performed in the first PR (point B). Following the first PR there are two pairs of TPPS-PR. Each TPPS will tune the polarization phase in order to feed the PRs with the suitable polarization phase so that, at the output of the third PR (point F), the desired PER is achieved. The last TPPS then produces the appropriate polarization phase shift so that the desired SOP is obtained at the output (point G).

□ **Drawbacks of PR with thermo-optic effect:** Although, the design offers good trade-off between performance and size but still it is limited by the fact that thermal effect can induce phase shift in other waveguides due to cross-talk. This may occur when this system is used in commercial designs with high packing density.

**Tunable PR using Berry's phase:** Berry's phase is a quantum-mechanical phenomenon that may be observed at the macroscopic optical level through the use of an enormous number of photons in a single coherent state [58]. In the special case of planar (non-helical) paths, such as the paths typically taken by planar optical waveguides, no significant optical rotation is observed independent of the complexity of the path [59]. The key to manifest Berry's phase in photonic integrated circuits is

to introduce out-of-plane three-dimensional waveguides to create a two-dimensional momentum space with non-zero (Gaussian) curvature.

## □ Design: Tunable PR with Berry's phase

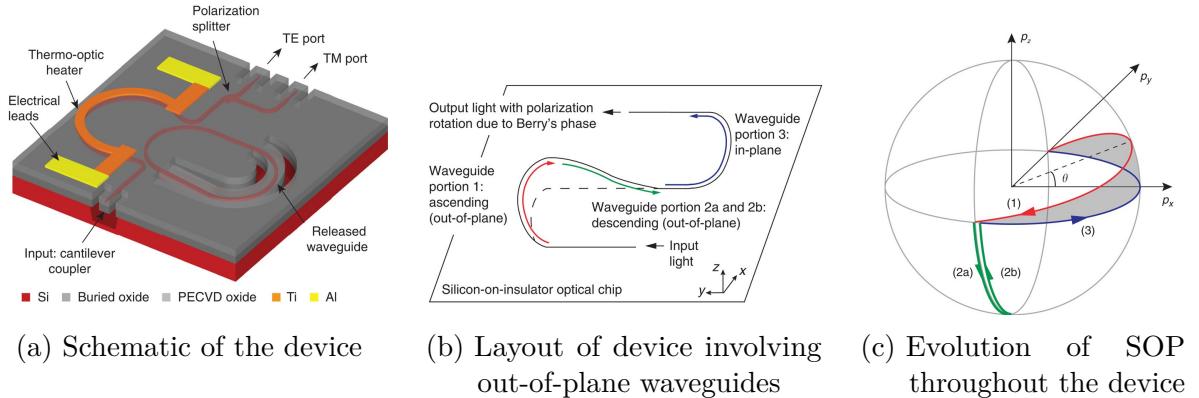


Figure 2.18: PR control using three PR and three TPPS, by Xu *et al.* [37]

Monochromatic light at wavelength  $\lambda$  carries a momentum given by  $p = p_x\hat{x} + p_y\hat{y} + p_z\hat{z} = \hbar k$ , where  $k$  is the propagation vector, with magnitude  $2\pi/\lambda$  and  $\hbar$  is the Planck's constant divided by  $2\pi$ . In physical space, the layout consists of three main portions. The first portion, shown in red in Fig. 2.18b, consists of an ascending out-of-plane  $180^\circ$  waveguide bend. The second portion, shown in green, consists of an out-of-plane waveguide that descends to the chip surface. Finally, the third portion consists of an in-plane  $180^\circ$  bend. In momentum space, the corresponding paths for each waveguide portion are shown in Fig. 2.18c using Poincaré sphere (2.1.8). Light propagation along the three-dimensional path in physical space results in a non-zero subtended solid angle in momentum space, shown as the shaded area in Fig. 2.18c. Therefore, the waveguide geometry will exhibit Berry's phase. A change in wavelength results in a change of the radius of the sphere in momentum space but not the solid angle. If the deflection angle of waveguide portion 1, in the physical space shown in Fig. 2.18b is  $\theta$ , then the output light will appear with polarization rotation equal to  $2\theta$  due to Berry's phase because the magnitude of the solid angle extended by the grey area in momentum space, shown in Fig. 2.18c, is  $\theta$  [37].

- **Drawbacks of PR using Berry's phase:** This device uses out-of-plane ring cavity which uses the principles of ring resonator. The ring resonator is limited by its narrow band spectral features which limits bandwidth. Also, the device uses a non-birefringent waveguide, which is lossy in terms of photonic substrate, as an oxide cladding is used to confine light.

### 2.2.2.3 Other Polarization tuning mechanisms

**Thermal tuning:** Thermal tuning mechanisms rely on the thermo-optic effect of materials, where their RI changes with temperature. In silicon, the thermo-optic coefficient

$(dn/dT)$  around 1550 nm and 300 K is about  $+1.8 \times 10^{-4} K^{-1}$ . Above room temperature, this coefficient increases with a weak quadratic dependence. Similarly, the thermo-optic coefficient of materials such as InP, GaAs, and SiC also increase quadratically with temperature.

**Electro-optic mechanism:** Electro-optic effects refer to changes in the optical constants of a material due to an applied electric field, and are broadly divided into changes in absorption or RI. They do not involve carrier injection or depletion. Electro-absorption refers to a change in the absorption of a material due to an applied electric field. Other effects, such as the Pockels effect, explain the change in the RI of a material with an applied electric field. The Pockels effect is linear with the electric field, but is only observed in materials that lack inversion symmetry (hence, not in silicon). Electro-optic effects have been realized using III–V materials through micro-disks and micro-rings. However, only moderate resonant wavelength shifts are achieved [60].

**Liquid crystals mechanism:** Nematic liquid crystals (NLC) are materials that flow like a liquid but have their molecules oriented as a solid crystal. NLC are birefringent, i.e., they have a RI that is dependent on the polarization and direction of propagation of light. In the presence of an electric field, the NLC molecules align themselves along the field lines. This changes the polarization of the light passing through it, and therefore changes its RI. It is therefore possible to achieve electrically tunable optical devices based on NLC [61].

**Free carrier plasma dispersion effect:** The injection of free carriers into a material causes a change in its RI. This effect is known as the plasma dispersion effect. The free carriers are generated by single- or two-photon absorption from a pump laser, or injected through forward bias of a p-i-n junction. Alternatively, free carriers can be depleted from a previously doped region. The change in the free carrier concentration will therefore affect the optical properties of the material. When carriers are injected into an intrinsic region, the electron–hole pair density increases, which decreases the effective index [62].

**Opto-mechanical tuning:** Opto-mechanical tuning refers to the integration of MEMS with photonic devices. When applied to micro-resonators, the evanescent field of the resonant mode can be externally perturbed, either from the top or from the side. Two effects may result as a consequence of such perturbation: change in the effective index of refraction of the mode inside the resonator (since the evanescent tail of the mode sees a different cladding), and increase in the optical loss due to coupling/absorption of the propagating mode into/by the perturbing structure. Coupling ratios between bus waveguides and micro-resonators can also be modified through mechanical movement of suspended bus waveguides, normally needed for post-fabrication tuning or trimming [60]. Opto-mechanical tuning by electrostatic actuation can potentially provide a broad wavelength tuning range, while requiring low energy for operation.

# 3 Chapter 3

# Design and simulation

TPR can be achieved in different ways, discussed in section 2.2.2.2. In this thesis, the goal is to achieve TPR using MEMS for a broadband spectrum including C and L bands. Moreover, the idea is to optimize the design to achieve high PER and low IL.

## 3.1 Approach

MEMS TPR can be approached in 2 ways. In a first approach, initially a passive PR can be designed by introducing asymmetry and another MEMS tunable waveguide is introduced which impedes polarization rotation by reintroducing symmetry in the effective waveguide. In a second approach, the technique is reversed i.e. the MEMS tunable waveguide is used to introduce asymmetry in the waveguide structure which rotates polarization. Without the MEMS structure the polarization is not rotated. In the design principle of the TPR described here, the first approach is being followed.

## 3.2 Designing TPR

To design the geometry of the waveguide standard mode solver softwares are used. Both, Comsol[63] and CST [64] are used to solve the modes in equation 2.19. Mostly, in this thesis Comsol is used to find and optimize the port modes in 2-D geometry. Whereas, CST is used to optimize the 3-D structure by studying the transmission parameters (S-parameters).

### 3.2.1 Design principle

To design a PR in nanometer scale, precision is a key factor. Index profile of chosen silicon can also affect the structural dimensions of the design in a rigorous manner. Meshing of the geometry, cladding dimensions and its material composition, frequency domain of the solvers etc. are the key things to watch for in designing the simulation in the mode solver softwares. As the idea is to make the TPR as broadband as possible, it is necessary to do frequency analysis simulation for a wide-band spectrum in which the optical fibers for telecommunications work. As the operating wavelength of the

telecommunications optical fiber network in C-band and L-band are between 1530 nm and 1625 nm, the corresponding frequency domain becomes 184.48 THz - 195.94 THz.

### 3.2.2 Design A: Single stair Si waveguide on SOI with air cladding based on mode hybridization

Initially, a single stair waveguide is being designed for PR. To find out the dimensions for obtaining 45° hybridized modes, Comsol 2D mode solver is used.

#### 3.2.2.1 Waveguide geometry

Throughout the next sections the dimensions of the stair waveguide are defined in terms of rib, slab and base described in Fig. 3.1.

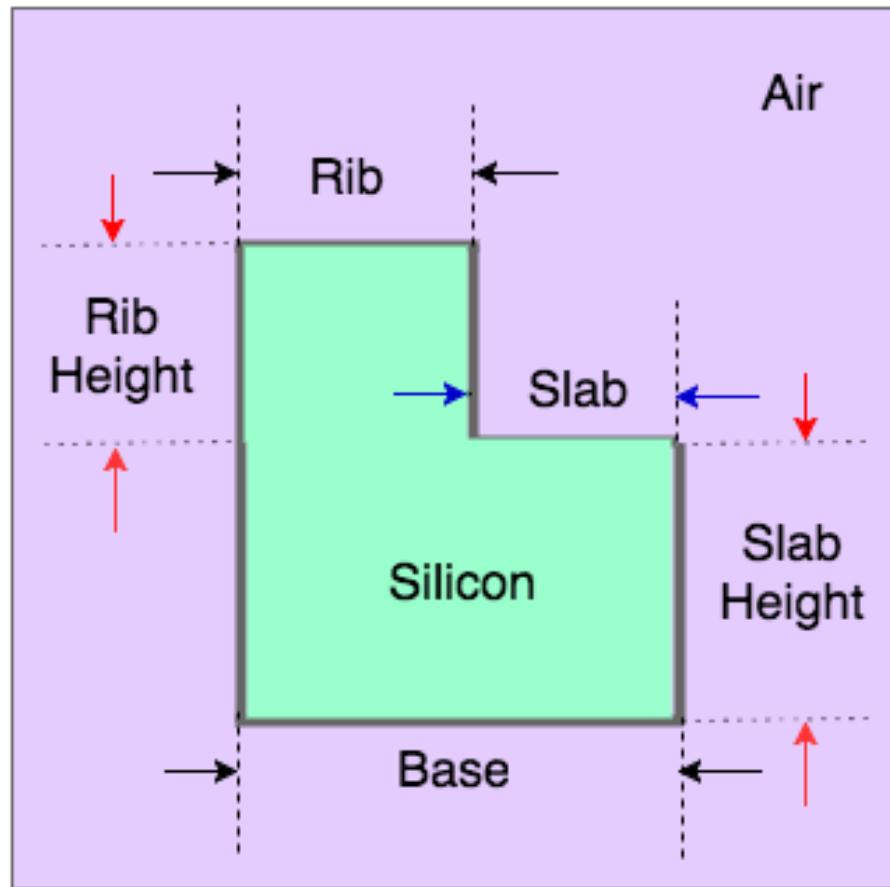


Figure 3.1: Stair waveguide geometry

#### 3.2.2.2 Optimized dimensions of primary PR waveguide

At 45°, the components of the E-fields in the hybridized modes must be such that,  $E_X \approx E_Y$ . Hence,  $\frac{\text{Avg}(E_{X_{\text{mode}}})}{\text{Avg}(E_{Y_{\text{mode}}})} \rightarrow 1$ . As a result,

$$\sum_{mode} Real \left| \log_{10} \frac{Avg(E_{X_{mode}})}{Avg(E_{Y_{mode}})} \right| \rightarrow 0. \quad (3.1)$$

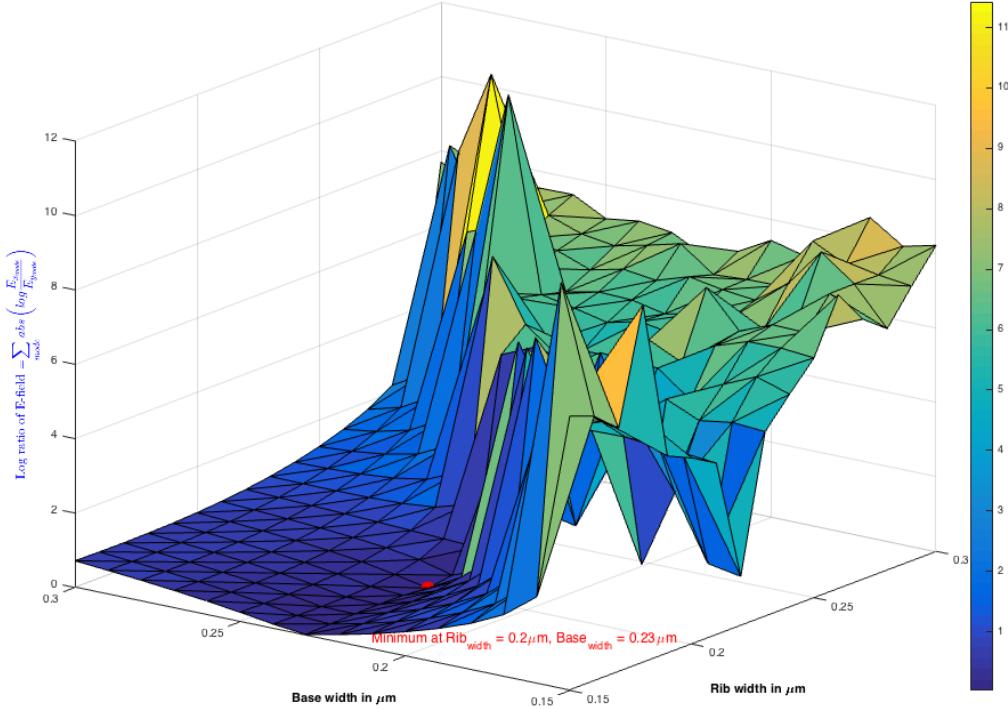


Figure 3.2: Summation of real part of absolute value of the logarithmic ratio of  $E_x$  and  $E_y$  fields plotted against rib and base width in an area chart using MATLAB

Hence, the minimum point on the graph represents the best dimensions on the waveguide for obtaining the hybridized modes at  $45^\circ$ . In this case the best dimensions were obtained at  $\text{Base}_{\text{width}} = 230\text{nm}$  and  $\text{Rib}_{\text{width}} = 200\text{nm}$ . The total height of the waveguide is 220nm and the  $\text{Slab}_{\text{height}} = 110\text{nm}$ . It can be visualized that in the modes in Fig. 3.3a and Fig. 3.3b, that the effective modes are hybridized at  $45^\circ$  for the first 2 hybrid modes obtained using Comsol simulation. It is necessary to double check the E-fields orientation to make sure that only the correct modes are chosen because in simulation a larger cross-section than the waveguide cross-section is excited. This excitation might produce modes for which the equation 3.1 satisfies but the modes are not hybridized at  $45^\circ$ . Lastly, the height in the geometry is chosen around 110nm for the current limitation of the dry-etch step in the fabrication process present in the lab. A double stair waveguide could also have been chosen, but that would increase the fabrication steps.

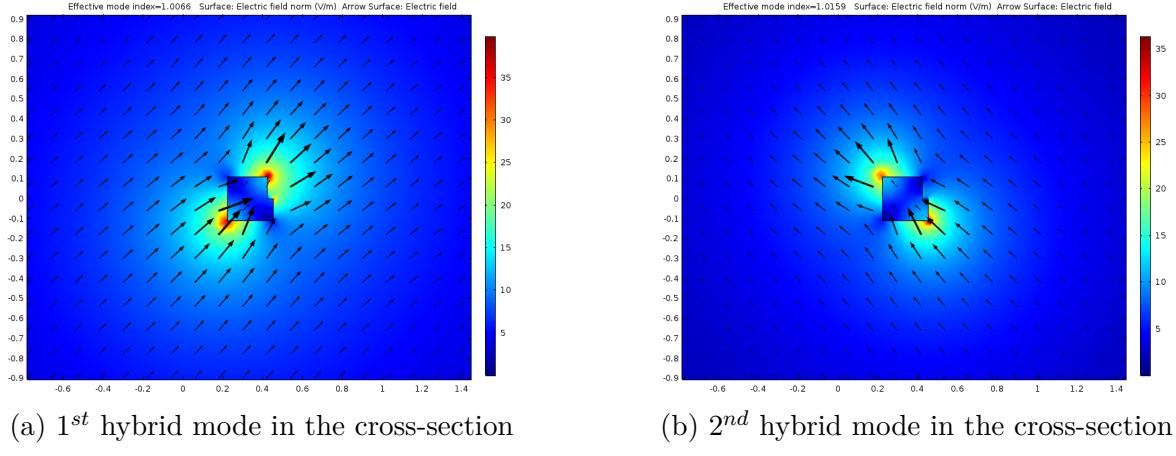


Figure 3.3: Fundamental hybrid modes in the cross-section with  $\text{Rib}_{\text{width}} = 200\text{nm}$ ,  $\text{Rib}_{\text{height}} = 110\text{nm}$ ,  $\text{Base}_{\text{width}} = 230\text{nm}$ ,  $\text{Slab}_{\text{height}} = 110\text{nm}$ , obtained using Comsol 2-D eigenmode simulation

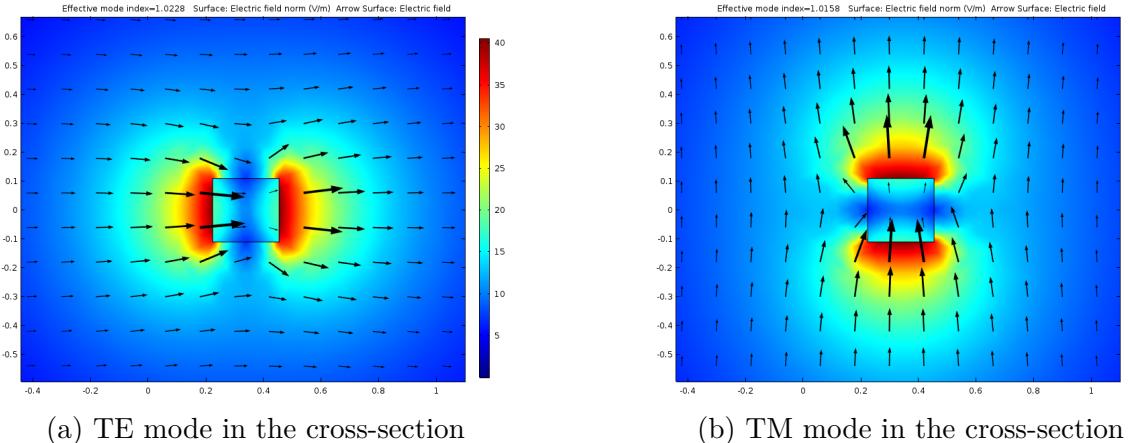


Figure 3.4: Fundamental modes in the cross-section with Width = 230nm, Height = 220nm, obtained using Comsol 2-D eigenmode simulation

Also, since the port dimensions are different from the cross-section dimensions it is necessary to check if the 2 fundamental modes can be supported by the ports. Hence, port mode simulation for the first two fundamental modes in waveguide with dimensions  $230 \times 220$  nm are calculated and the results obtained are displayed in Fig. 3.4a and Fig. 3.4b. This corroborates that the 2 fundamental modes TE and TM are supported in the ports.

Next, the effective RI for both the port modes are obtained using CST by doing a parametric sweep over the operating frequencies of C and L-band. The results are displayed in Fig. 3.5.

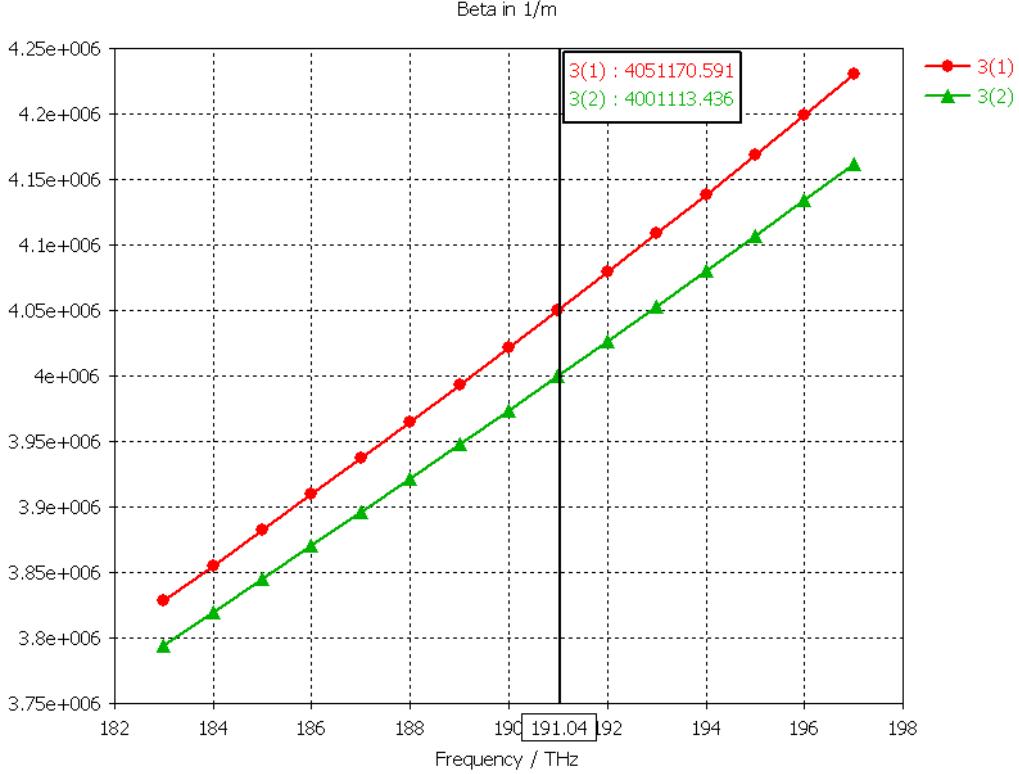


Figure 3.5: Simulated effective RI profile for the port modes in the cross-section of Rib<sub>width</sub> = 200nm, Rib<sub>height</sub> = 110nm, Base<sub>width</sub> = 230nm, Slab<sub>height</sub> = 110nm, obtained using CST 3-D simulation

The required length of the cross-section is obtained using 2.30. Since,  $\beta_1 = 4.051 \times 10^6$  and  $\beta_2 = 4.001 \times 10^6$ . Hence,  $L = \frac{\pi}{\beta_1 - \beta_2} \approx 51\text{nm}$ . This means the length of the stair cross-section would be around 51nm. Effective RI is dependent on frequency and so the cross-section length is also dependent on the frequency. The length is calculated at around 191 THz, so that the whole of the band (184.48 THz - 195.94 THz) can be covered for a relative good performance. This results could have also been obtained from COMSOL from the effective RI calculation as shown in 3.2.

$$L_\pi = \frac{\pi}{\beta_1 - \beta_2} = \frac{\pi}{2\pi(n_1 - n_2)} = \frac{\lambda}{2(n_1 - n_2)} \quad (3.2)$$

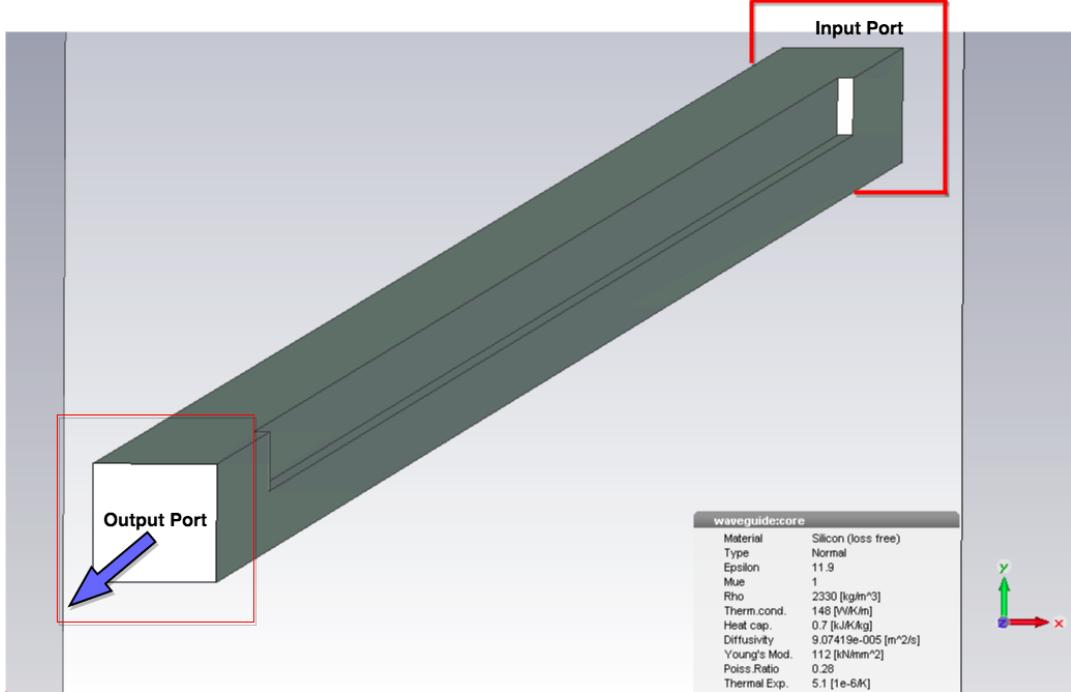


Figure 3.6: Design of single-stair waveguide with initial dimensions at the port as width = 230nm and height = 220 nm. Stair cross-section dimensions are: Rib<sub>width</sub> = 200nm, Rib<sub>height</sub> = 110nm, Base<sub>width</sub> = 230nm, Slab<sub>height</sub> = 110nm, and cross-section length = 51  $\mu$ m. The output port is along the Z-axis, shown in the figure

The 3D-design is simulated in CST with air cladding and with the previously estimated dimensions. The input and output ports are defined on the waveguide, which supports the two fundamental modes. As shown in Fig. 3.6, the stair cross-section can be envisaged if a Z-plane is cut in the asymmetric part of the waveguide.

Next, the S-parameters of the design are verified. The S-parameter is being labelled as follows,

$$SA(M), SB(N), \quad (3.3)$$

where A=output port, B=input port and M,N = mode number. For example, S2(2),S1(1) means that input port is 1 and the mode is 1 whereas, output port is 2 and the mode at the output port is 2. Hence, S2(1),S1(2) and S2(2),S1(1) needs to be checked along with S2(1),S1(1) and S2(2),S1(2) for calculating the PER. The S-parameters obtained from the simulation shown in Fig. 3.7 (for, 200nm  $\times$  230nm) verifies that the model works according to the design principle with good PER over the whole band.

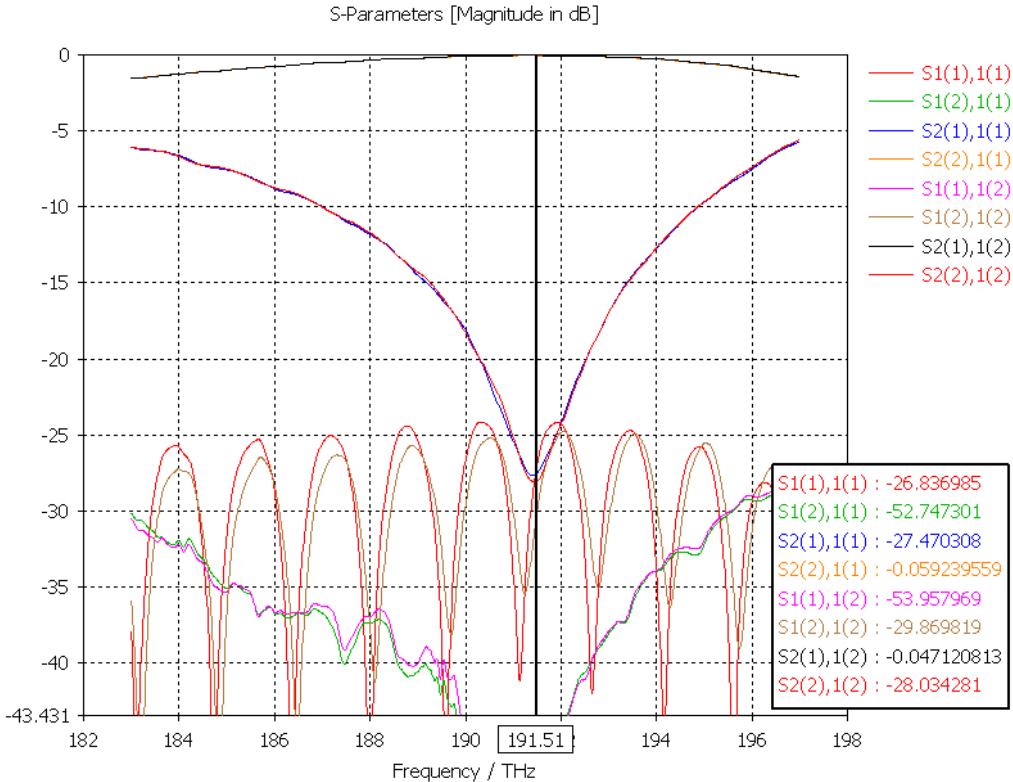


Figure 3.7: Simulated S-parameters in the single-stair waveguide with initial dimensions at the port as width = 230nm and height = 220 nm. Stair cross-section dimensions are: Rib<sub>width</sub> = 200nm, Rib<sub>height</sub> = 110nm, Base<sub>width</sub> = 230nm, Slab<sub>height</sub> = 110nm, and cross-section length = 51  $\mu$ m obtained using CST 3-D simulation

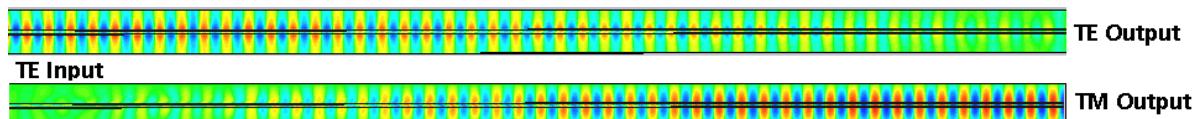


Figure 3.8: TE to TM mode conversion view from top perspective

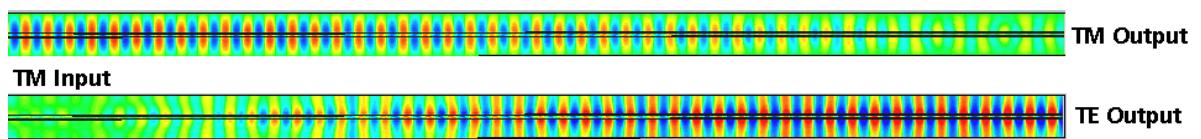


Figure 3.9: TM to TE mode conversion view from top perspective

### 3.2.2.3 Optimized dimensions of secondary MEMS waveguide

After finding the dimensions of the passive PR, the design of the MEMS tunable waveguide was designed to neglect the effect of rotation. Intuitively, if any waveguide which is the mirror image of the bus waveguide is place along side the bus waveguide, then PR effect would be nullified. This is verified by plotting the graph in Fig. 3.10. Since, at TE or TM mode,  $E_X \gg E_Y$ , or  $E_Y \gg E_X$ . Hence,  $\left| \frac{\text{Avg}(E_{X_{\text{mode}}})}{\text{Avg}(E_{Y_{\text{mode}}})} \right| \rightarrow \infty$ , or  $\left| \frac{\text{Avg}(E_{Y_{\text{mode}}})}{\text{Avg}(E_{X_{\text{mode}}})} \right| \rightarrow \infty$ , depending on TE or TM-mode. Hence,

$$\sum_{\text{mode}} \text{Real} \left| \log_{10} \frac{\text{Avg}(E_{X_{\text{mode}}})}{\text{Avg}(E_{Y_{\text{mode}}})} \right| \rightarrow \infty, \quad (3.4)$$

and the maximum points on the graph will represent the dimensions of the MEMS structure for which, there is no PR. Logarithmic scale is used to plot the data in a manageable way. The supermodes are also verified in the cross-section in Fig. 3.11a and Fig. 3.11b to make sure higher order modes are not supported.

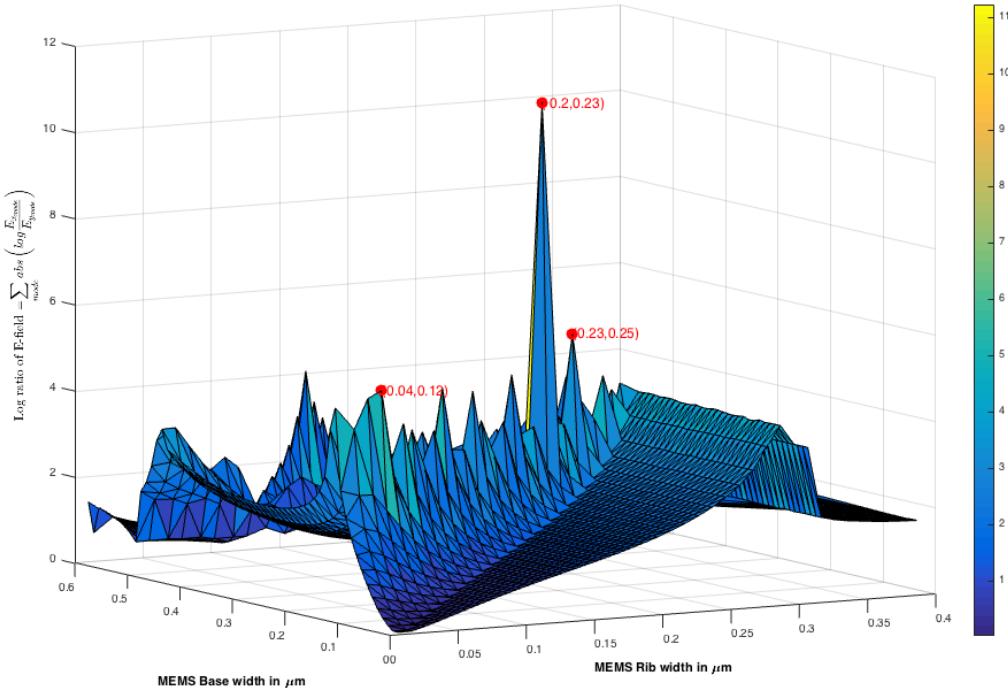
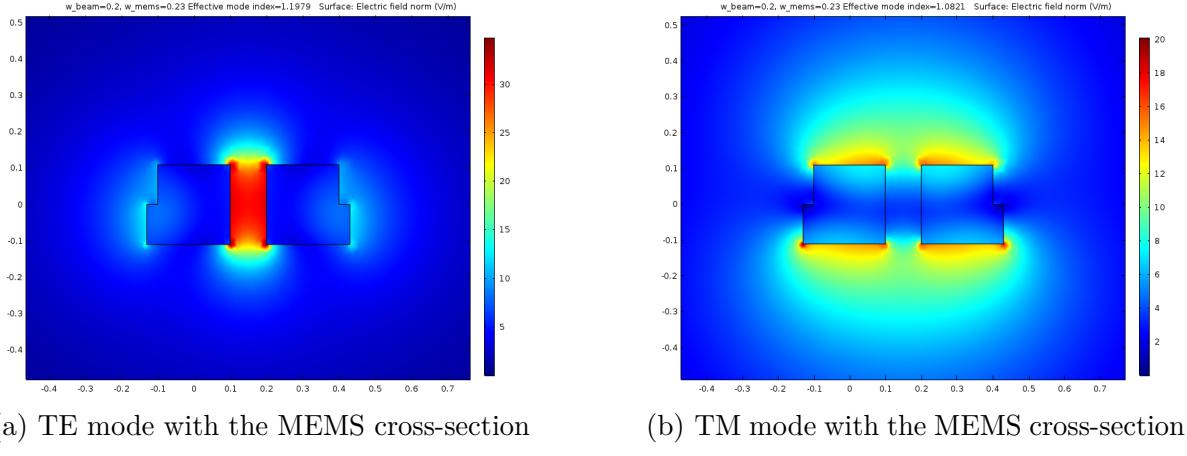


Figure 3.10: Summation of real part of absolute value of the logarithmic ratio of  $E_x$  and  $E_y$  fields plotted against rib and total width in an area chart using MATLAB



(a) TE mode with the MEMS cross-section

(b) TM mode with the MEMS cross-section

Figure 3.11: Modes in the cross-section with  $\text{Rib}_{\text{width}} = 200\text{nm}$ ,  $\text{Slab}_{\text{width}} = 30\text{nm}$ ,  $\text{Slab}_{\text{height}} = \text{Rib}_{\text{height}} = 110\text{nm}$ , in both bus and MEMS waveguide, obtained using Comsol 2-D simulation

In this case the best dimensions for the MEMS waveguide comes out as,  $\text{Rib}_{\text{width}} = 200$  nanometer,  $\text{Rib}_{\text{height}} = 110$  nanometer,  $\text{Base}_{\text{width}} = 230$  nanometer,  $\text{Slab}_{\text{height}} = 110$  nanometer. Fig. 3.11a and Fig. 3.11b, obtained using Comsol 2D simulation displays the port modes in the cross-section. This corroborates the claim that the MEMS waveguide must be mirror image of the bus waveguide to inhibit PR.

### 3.2.2.4 Representational design based on simulation

Based on the simulations performed and the dimensions of the cross-section obtained the tunable PR was designed as depicted in Fig. 3.12. However, for quicker simulation purposes the remaining portions of the MEMS waveguide cantilever are not considered in the simulation design.

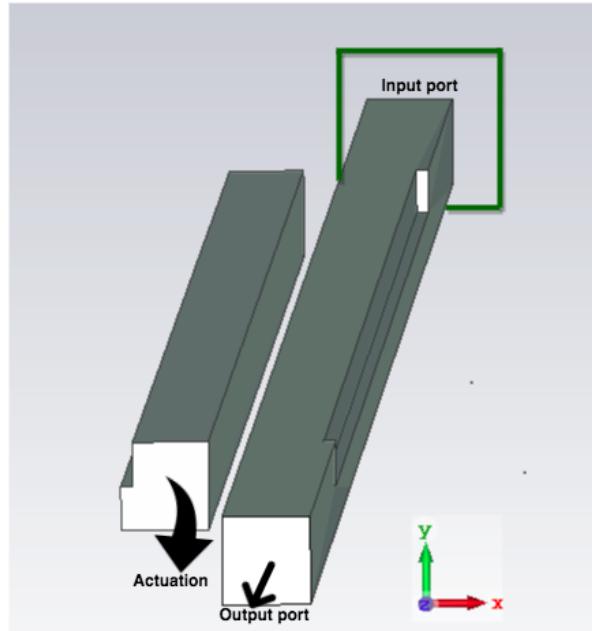


Figure 3.12: Design of single-stair waveguide with MEMS tuning waveguide. Stair cross-section dimensions are:  $\text{Rib}_{\text{width}} = 200\text{nm}$ ,  $\text{Rib}_{\text{height}} = 110\text{nm}$ ,  $\text{Slab}_{\text{width}} = 230\text{nm}$ ,  $\text{Slab}_{\text{height}} = 110\text{nm}$ , and cross-section length =  $51 \mu\text{m}$ , in both the PR waveguide and MEMS waveguide. The output port is along the Z-axis

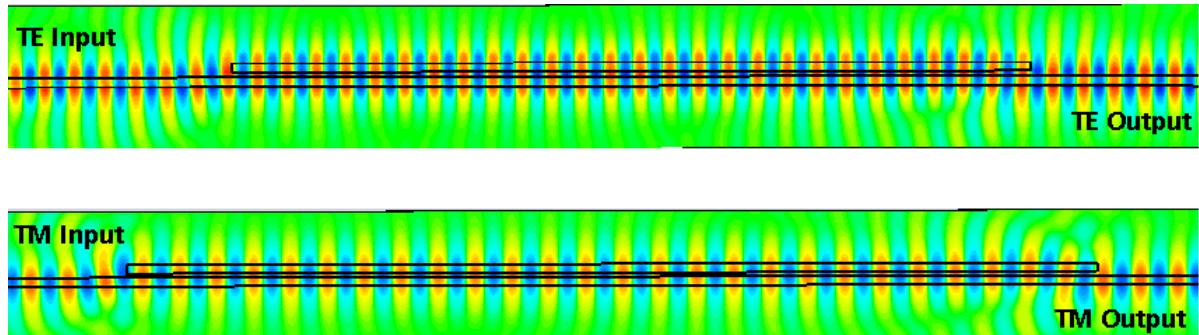


Figure 3.13: TPR transmission in silica cladding without MEMS waveguide actuation

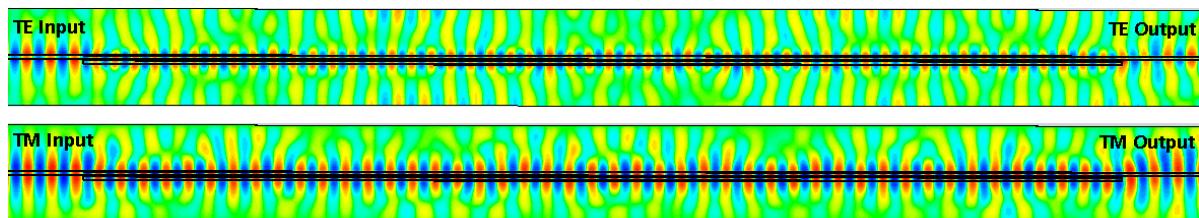


Figure 3.14: TPR transmission in air cladding without MEMS waveguide actuation

### 3.2.2.5 Device tolerance

When fabricating devices in nanometer scale often it is very difficult to control the device dimensions precisely. Hence, a brief study on simulation level is performed to check for deviance resulting due to variations in etch depth during the fabrication process discussed later in section 4.2.

Since the wafer used in the fabrication process is of height 220nm, the different etch depths considered are 100nm and 130nm which corresponds to 120nm and 90nm slab height respectively. First 20 minimum values of  $\sum_{mode} \text{Real} \left| \log_{10} \frac{E_{X_{mode}}}{E_{Y_{mode}}} \right|$ , is plotted against Rib<sub>width</sub> and Slab<sub>width</sub> in the following figure in Fig. 3.15 for an etch depth of 100nm.

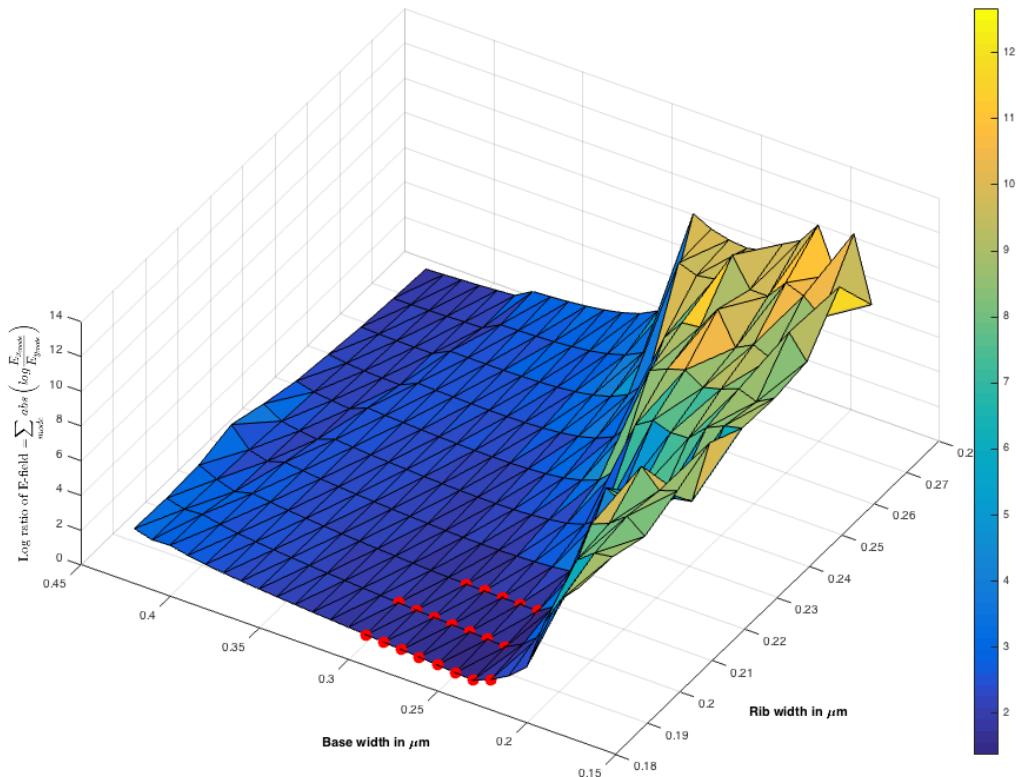


Figure 3.15: 20 least values, representing the summation of real part of absolute value of the logarithmic ratio of  $E_x$  and  $E_y$  fields, plotted against rib and total width in an area chart using MATLAB for Slab<sub>height</sub> = 120nm

It can be seen in the above Fig. 3.15 that the hybridized modes appear to be at 45° around  $230\text{nm} \leq \text{Base}_{\text{width}} \leq 300\text{nm}$  and  $180\text{nm} \leq \text{Rib}_{\text{width}} \leq 200\text{nm}$ . So, if the Rib<sub>width</sub>

and  $\text{Base}_{\text{width}}$  are controlled in the fabrication process, the device can still function and needs to be characterized accordingly.

The same process is followed for a speculated etch depth of 130nm and the 20 best dimensions are plotted which comes out to be  $230\text{nm} \leq \text{Base}_{\text{width}} \leq 300\text{nm}$  and  $160\text{nm} \leq \text{Rib}_{\text{width}} \leq 200\text{nm}$ . The exact pairs can be identified in the Fig. 3.16.

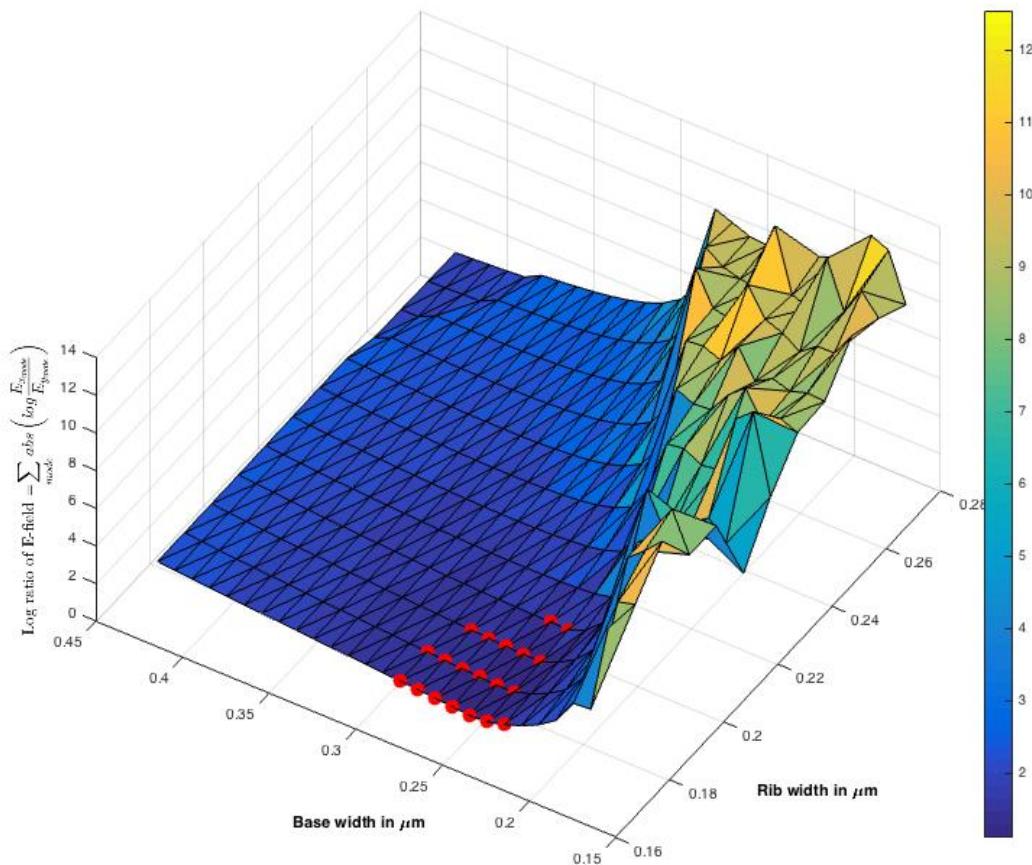


Figure 3.16: 20 least values, representing the summation of real part of absolute value of the logarithmic ratio of  $E_x$  and  $E_y$  fields, plotted against rib and total width in an area chart using MATLAB for Slab height = 90nm

### 3.3 Designing auxiliary components for measurement setup

To test the TPR auxiliary components like grating couplers (TE & TM), tapers, Polarization Beam Splitter (PBS) are designed. The gratings are designed in way to couple TE

and TM-modes from the LASER to the waveguide taper. The tapers are connected to the TPR, to reduce the mode size. Finally, a PBS is designed which again decouples the TE and TM-modes to the grating couplers via tapers where a photo-detector measures the intensity of output light. Another approach like butt-coupling can be used. But it is difficult to couple light into narrow waveguides in a low-loss manner as the mode size is bigger.

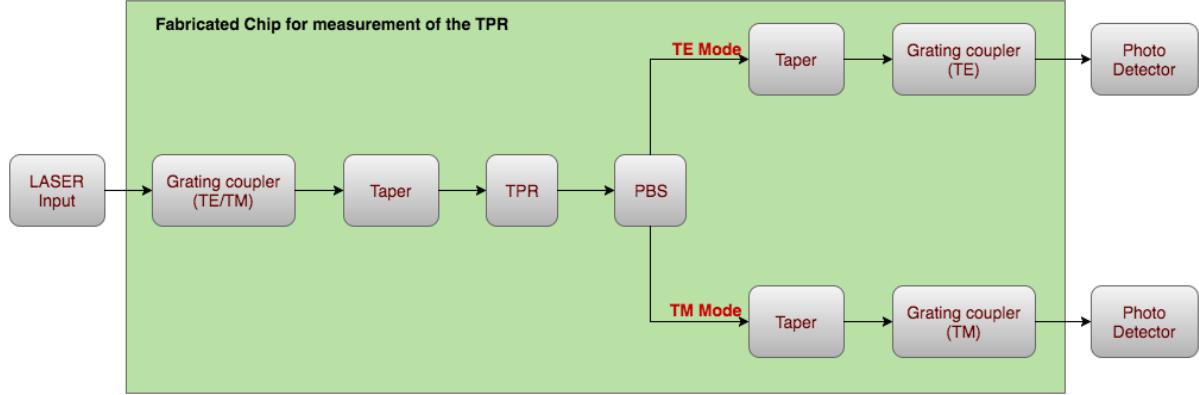


Figure 3.17: System level block diagram of the fabricated measurement setup

In the Fig. 3.17 a high level block diagram of the measurement setup is shown. Whereas, in Fig. 3.18 top view of the low level system design is shown with gratings, tapers, TPR, TM coupler and bridges.

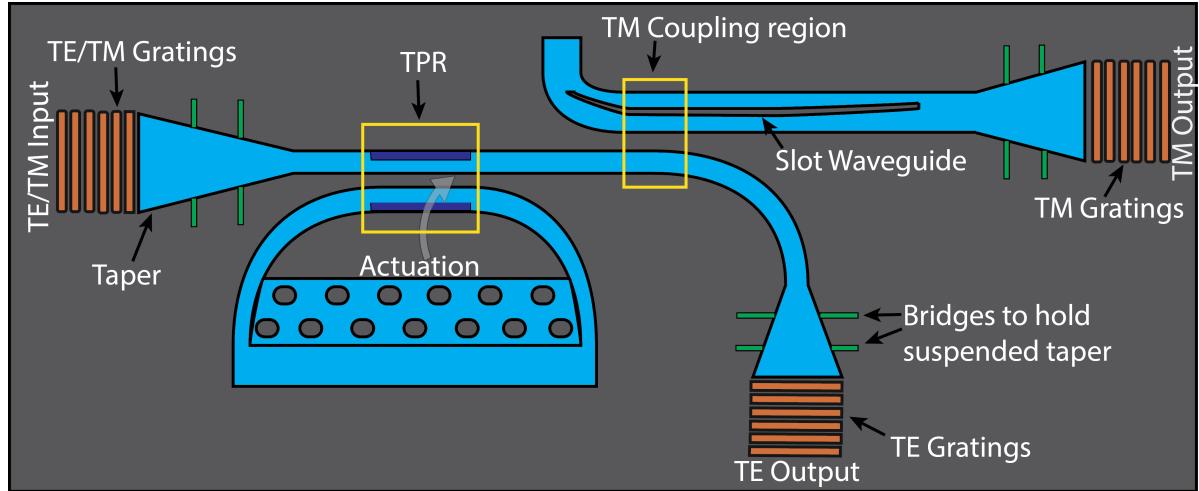


Figure 3.18: Low level schematic representation of the fabricated measurement setup

### 3.3.1 Grating coupler design

The high effective index and small mode dimensions of single mode silicon waveguides makes fiber coupling challenging. Waveguide-to-fiber surface grating couplers with fill

factor apodization offer low back reflection into the silicon waveguide and a single required lithography step. Using surface grating couplers, the mode matching problem can be solved by expanding the width of the on-chip silicon waveguide, and etching a grating into the expanded section that diffracts light out of plane into a fiber placed normal to the surface. The approach taken increases the coupling efficiency by tailoring the leakage factor of the grating to the mode profile of the fiber. The main benefits of this approach are a low back reflection into the silicon waveguide and high efficiency in the coupling [65]. In the design, the gratings used are 1200 nm wide which narrows down to a width of 230 nm in the PR section. The approach is shown in Fig. 3.19a.

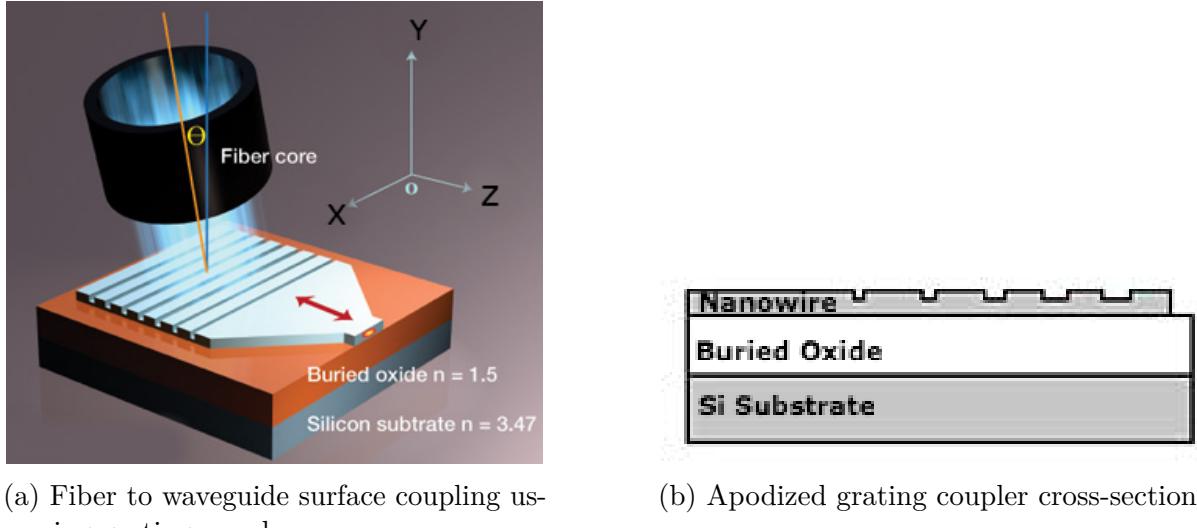


Figure 3.19: Overview of surface coupling from fiber to waveguide using apodized grating coupler with cross-sectional view

### 3.3.2 Taper with slab design

While tapering down to the TPR cross-section from the grating coupler cross-section, the  $\text{SiO}_2$  underneath is etched away. Hence, to support the structure from the side bridges are drawn which forms a slab like structure at certain cross-sections. These kinds of structures accommodate mode conversions between  $TM_0$  and  $TE_3$ . Also, these bridges can be used in different places in the test structure where support is necessary to hold the waveguide. For example, if the core waveguide width is 700 nm then a total base width (base and slab) of 1500 nm must be avoided for mode conversion reasons. This is simulated using COMSOL and the results are plotted in Fig. 3.20. As, it can be seen that around 1500 nm base width there is a mode conversion between  $TM_0$  and  $TE_3$  represented in Fig. 3.21a and Fig. 3.21b.

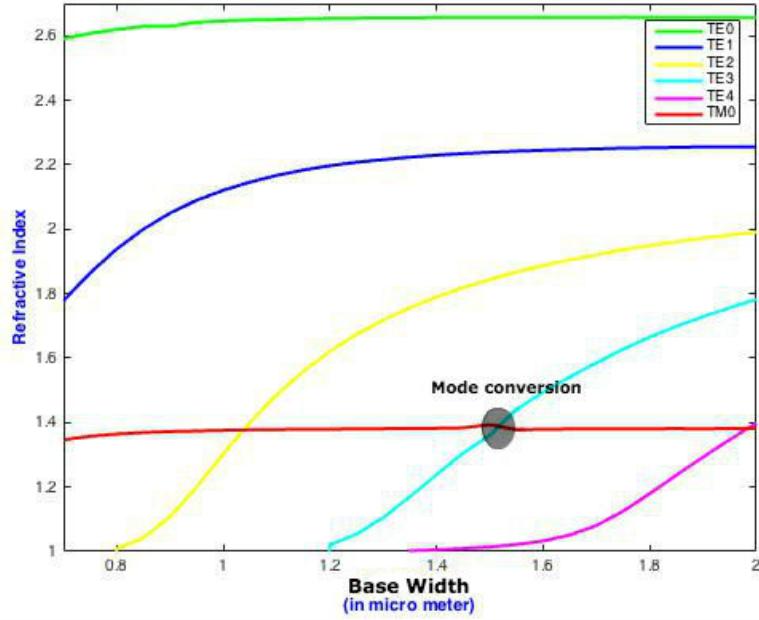


Figure 3.20: TE and TM modes at different base widths obtained using COMSOL mode solvers

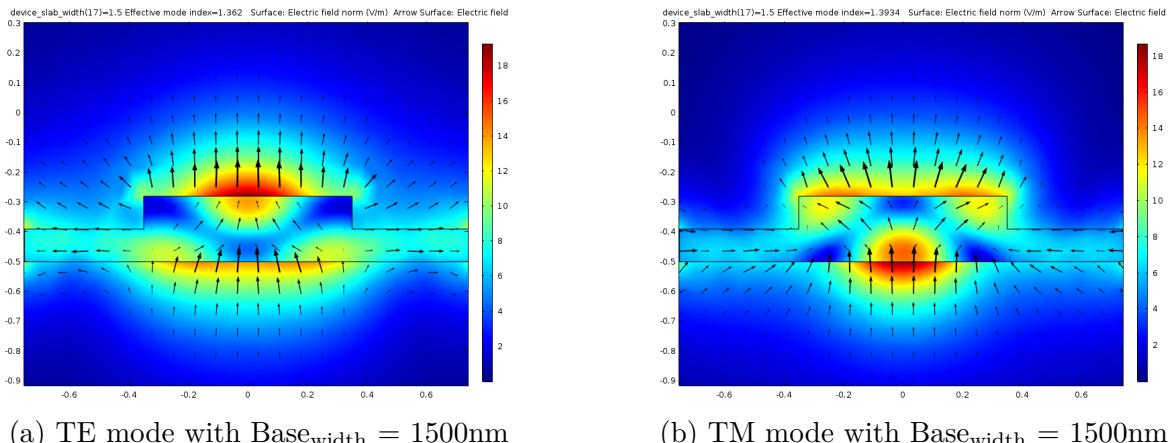


Figure 3.21: Mode conversion in Slab modes at  $\text{Base}_{\text{width}} = 1500\text{nm}$ , obtained using Comsol 2-D simulation

### 3.3.3 Polarization beam splitter design

The PBS is based on an asymmetrical directional coupler by utilizing the evanescent coupling between a strip-nanowire and a nanoslot waveguide [66]. First, RI is calculated for different core widths with height = 220nm. The results are displayed in Fig. 3.22.

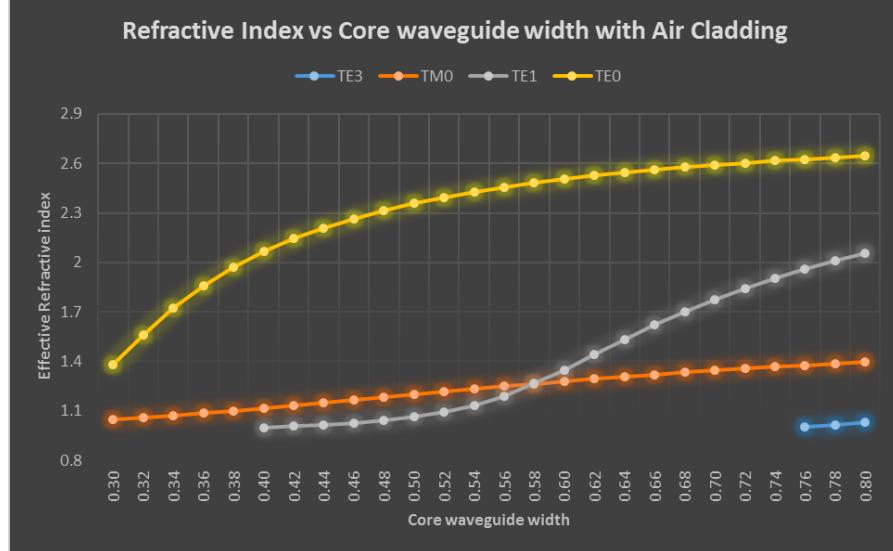


Figure 3.22: RI for different dimensions of core waveguide width

Next, the RI is calculated for different widths of nanoslot waveguide with a height of 220nm and slot width of 100nm. The gap between the strip-nanowire and the nanoslot waveguide is 150nm. The results are plotted in Fig. 3.23.

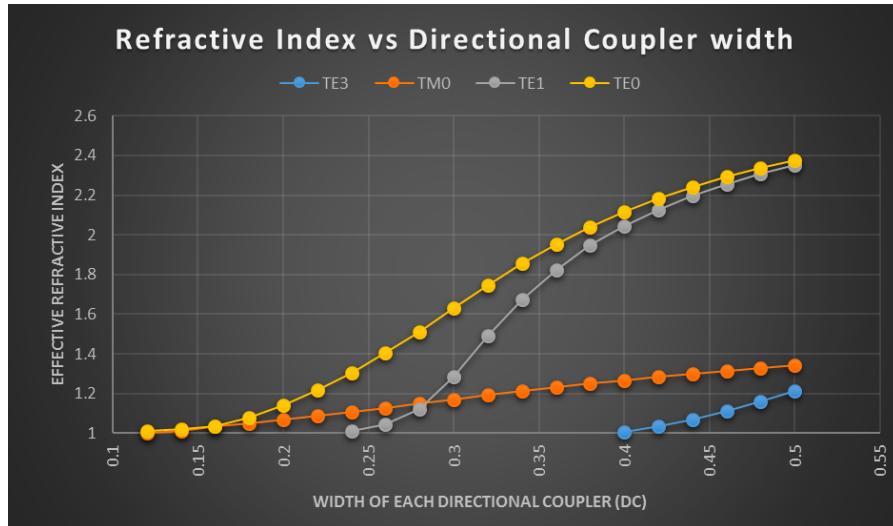
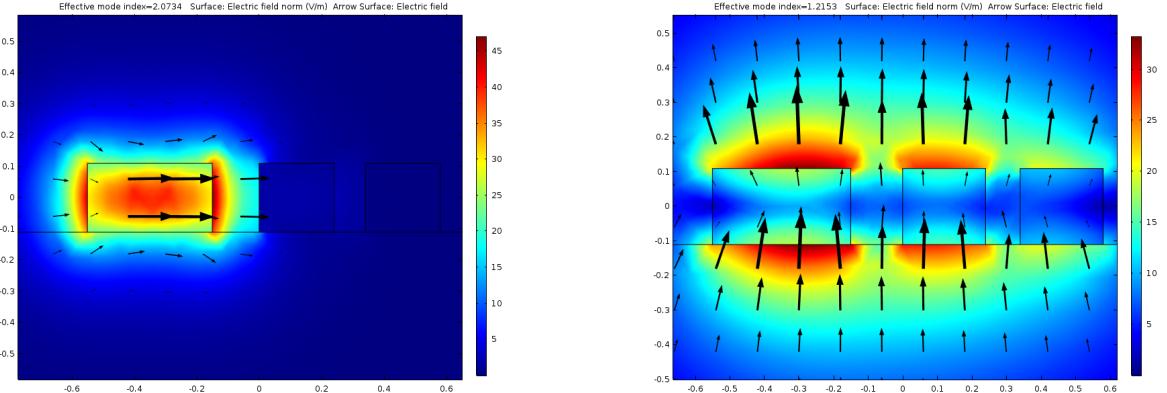


Figure 3.23: RI for different dimensions of slot cross-section

It can be seen in Fig. 3.22 that the effective index of  $TM_0$  at a width of 500nm is 1.20. Whereas, it can be seen in Fig. 3.23 that the effective index of 1.20 in  $TE_1$  is obtained around a width of 330nm for each section of the nanoslot waveguide. Also, the supermodes are checked in the cross-section keeping the strip-nanowire and the nanoslot waveguide to understand the coupled modes shown in Fig. 3.24a and Fig. 3.24b.



(a) TE coupling in the mode coupling cross-section

(b) TM coupling in the mode coupling cross-section

Figure 3.24: TE and TM coupling in PBS slot waveguide at the mode coupling region

Finally, the designed is simulated in 3-D using CST for checking the transmission with strip-nanowire of width 500nm and nanoslot waveguide of width 330nm each with slot width of 100nm. The coupling length is estimated from 3.2. As,  $n_{TE0} = 2.35$  and  $n_{TM0} = 1.20$ , hence  $L_\pi = 1.4 \mu\text{m}$ . As seen in Fig. 3.25a, the TE mode goes through the without coupling. Whereas, as seen in Fig. 3.25b, the TM mode crosses through in the coupling region. As, it can be seen some portion of the TM mode goes through as well. However, the measured PER is more than 15dB. The purpose of this setup is to make sure that both TE and TM modes can be measured at different ports. In the final design of the measurement setup the nanoslot waveguide is not bend after the coupling region to minimize losses for TM mode. As TM mode is highly deconfined, bends can cause lossy transmission for TM modes. Whereas, sine TE mode is confined the strip-nanowire core waveguide is given a sharp bend to minimize coupling beyond the coupling region. The idea can be viewed in Fig. 3.18.

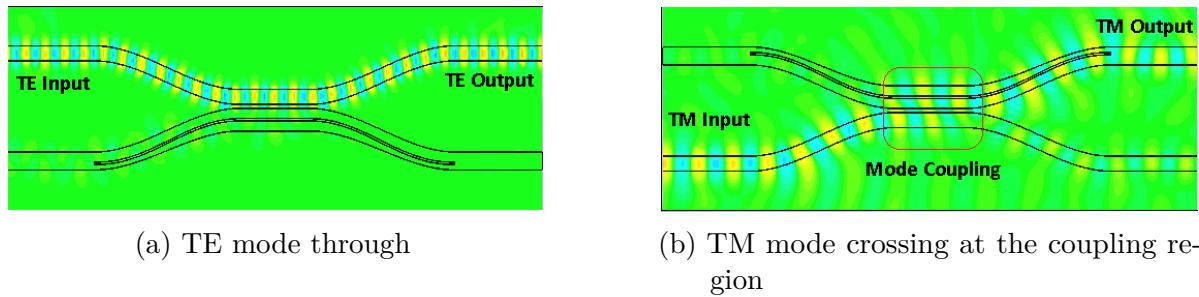


Figure 3.25: PBS with TM coupling due to mode matching using a slot waveguide

# 4 Fabrication

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Chapter 4

## 4.1 Unit tests

To fabricate the design in the clean-room in a precise manner various tests are performed. The tests in the fabrication iterations helps to improve the design in each iteration. The strategy followed resembles similarity to unit tests where each of the components are tested and verified to understand the design.

The test cases followed during the fabrication process are discussed below.

- Dose test:** The first test requires to verify the dose of Hydrogen silsesquioxane (HSQ) and ZEP7000 (ZEP) used in masking to prevent the damage of masked Si. For this different doses are applied on different portion of the chip by using similar CAD model.
- TE/TM—TE/TM grating with a normal waveguide:** To check any optical design it is necessary to couple the light into the chip with good transmission. That is why gratings are necessary. To check PR design, it was necessary first to check the TE and TM transmissions. Hence, the first test case was to check the TE/TM grating with a normal waveguide. This give an idea of transmission parameters and the next results were referenced to this value. This test ensured that the gratings worked as intended.
- TE/TM—TE/TM grating with tapers:** The next test was to check the transmission parameters of the tapers, which was obtained by just putting the tapers end-to-end after the gratings from both ends. In this test it was made sure that there was good transmission in the tapers.
- TE/TM—TM/TE grating with taper, normal waveguide and PBS:** Next it was necessary to check the PBS design based on asymmetrical directional coupler, required for the characterization of the converted modes.
- TE/TM—TE/TM grating with taper and thinner waveguide:** Since, the PR was on a thinner waveguide of thickness 230 nm whereas the gratings had a thickness of 1200 nm, it was necessary to use tapers to connect the gratings to the PR section. But before checking the PR, it was necessary to check if the transmission in the Si nano wires. That is the reason why this test case was performed.

- **TE/TM Grating with PR and PBS:** Now that all the auxiliary components have been tested, the PR design was tested as well with PBS and TE/TM grating for different lengths with taper.
- **Cantilever actuation with separation strategy:** Since, the actuation is done by applying a voltage it is necessary to check that the cantilever actuates properly on applying voltage and does not stick after removal of voltage. This is done by segregating the cantilever portion from other parts of the chip so that other portions of the chip are not affected.
- **TE/TM Grating with PR, PBS, MEMS waveguide and actuation:** Finally, if all the previous tests have succeeded the final design is tested with all the components and characterized.

The goal of the unit test strategy was to find and understand any short-comings which might occur at nano-scale at any stage of the fabricated process.

## 4.2 Fabrication process

The MEMS tunable device was fabricated using a standardized two step dry etch process on Silicon on Insulator (SOI) for the silicon device layer (resulting in two heights) and a wet SiO<sub>2</sub> under-etch [67]. The first lithography step defines the asymmetric shape of the ridge waveguides. The second lithography step and the wet under-etch defines the slab sections and free standing cantilever. The cantilever is delimited by the fully etched slot waveguides, and its free suspended area is determined by the placement of etch holes. The details of the fabrication process steps are described in the following section.

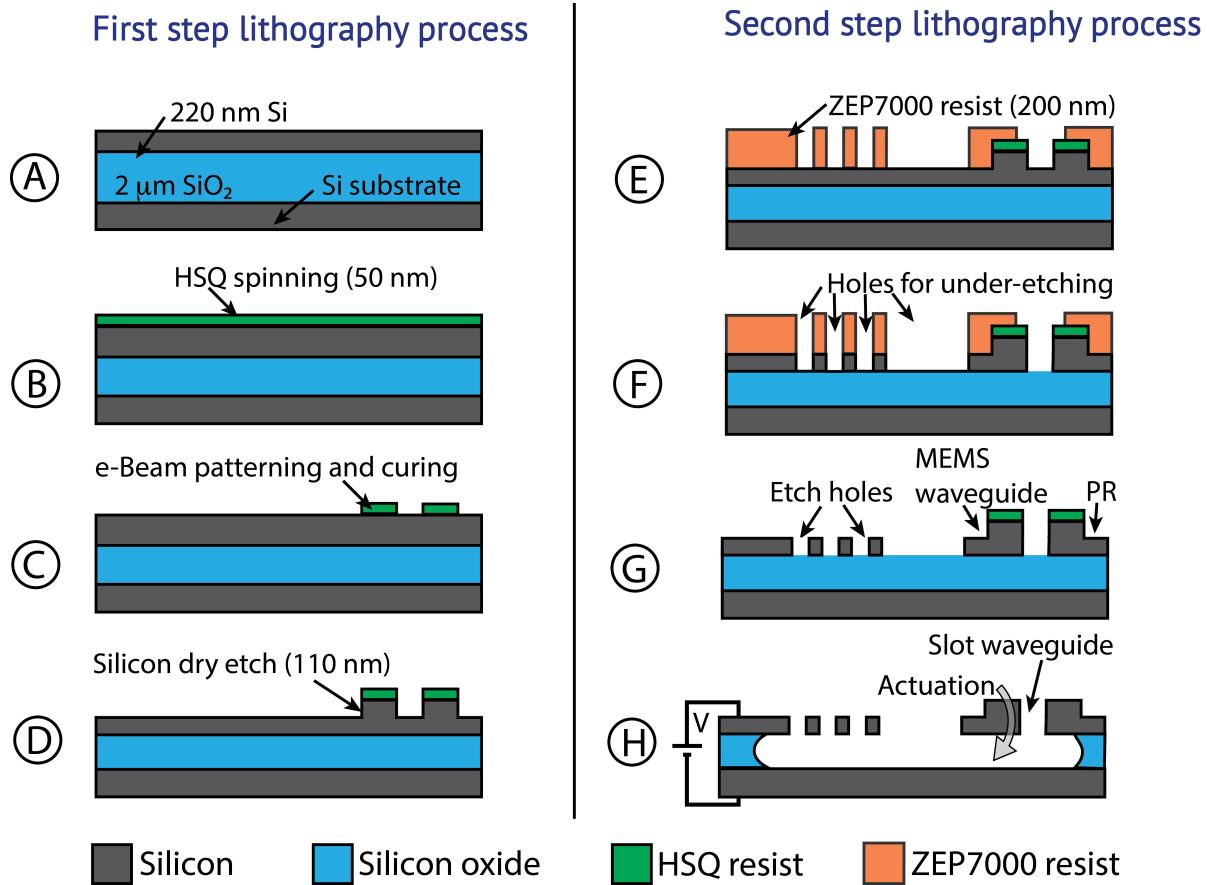


Figure 4.1: Cross-sectional schematic of the fabrication process

#### 4.2.1 Piranha bath

The fabrication process starts with cleaning the SOI chip with 220 nm crystalline silicon device layer and 2 μm buried oxide, in the piranha solution (Fig. 4.1 A). Piranha solution is a mixture of sulfuric acid ( $\text{H}_2\text{SO}_4$ ) and hydrogen peroxide ( $\text{H}_2\text{O}_2$ ), used to clean organic residues off substrates. Because the mixture is a strong oxidizing agent, it will remove most organic matter, and it will also hydroxylate most surfaces (add OH groups), making them highly hydrophilic (water-compatible) [68].

#### 4.2.2 HSQ resist spin

A HSQ negative resist is spun on the SOI chip to create a thickness of 50 nm. This is achieved by spinning the chip on a rotating platform at 4000rpm for 30 seconds. The HSQ layer is hardened by baking the chip on a hot plate at 170° C for 5 minutes. To measure the thickness of sample a scratch is made on the chip and checked for depth variations using mechanical profilometer (KLA-Tencor). This is done to verify the profile depth of the mask.

#### **4.2.3 First e-beam exposure**

To develop the chip, selective portions of the chip are exposed using e-beam. E-beam exposure exceeds patterning capability of optical lithography and creates patterns in sub-microns scale. Before loading the chip into the chamber via the sample stage, pressure is adjusted with the external environment. Initially, one corner of the chip is scratched to align the chip and find particles on the chip to focus the beam correctly. Write-field alignment is a very central adjustment in the process of getting the best possible e-beam lithographic result. It is the adjustment of the electromagnetic/electrostatic deflections system inside the column to the high precision X-Y-Z stage. The stage is considered to be “correct” and the e-beam deflection system is aligned to it. To increase the dose in certain portions of the chip (CAD drawn using Raith 150 e-beam lithography software), the scanning speed is slowed down so that more electrons can strike the HSQ surface and expose it with a higher dose. The chip is developed using ma-D 525 (micro-resist) which dissolves non-hardened HSQ. The chip is then put in water to dissolve ma-D 525 and dried using nitrogen. Finally, the exposed HSQ in the chip is hardened more by putting it in an oven for 40 minutes at 400° C. The chip is cleaned and covered with ceramic glass which avoids deposition of dust cloud. After this step the chip resembles the diagram in Fig. 4.1 C. Again mechanical profilometer is used to verify the thickness of HSQ.

#### **4.2.4 First dry etch step**

The device pattern is finally transferred to the device layer by a timed (HBr) dry etching of silicon ( $\approx 35$  seconds), resulting in ridge waveguides with 110 nm height on a 110 nm thick silicon slab (Fig. 4.1 D). The patterned HSQ remains on the chip for the next lithography step. Finally, optical profiling is performed to find out the depth of the silicon etch. This process marks the end of the first step lithography process.

#### **4.2.5 ZEP7000 spin**

A ZEP7000 resist (positive) is applied on the chip by using an eppendorf pipette. To achieve a ZEP profile of 200 nm thickness the platform is rotated at 3000 rpm for 45 seconds. The sample is baked at 170° C for 3 minutes to make the ZEP layer harder. After this, a scratch is then made on the sample and the profile depth is measured using a mechanical profilometer (KLA-Tencor).

#### **4.2.6 Second e-beam exposure**

Before the second e-beam exposure, local axis alignment is needed because it is a two-step fabrication. Some unique and easily recognizable feature like plus symbol is selected as a mark, patterned in the first exposure. The contamination dots from the focusing is a good example. Write-field alignment is performed in all the cells manually for dimensional precision [69]. Since ZEP is a positive resist, the exposed portions are developed using

p-Xylene solvent and MIBK. After developing the chip, the cross-section looks like Fig. 4.1 E.

#### **4.2.7 Second dry etch step**

The double step device pattern is obtained in the device layer when all the remaining silicon is etched. This is done via another dry etch step similar to the previous one ( $\approx$  35 seconds). The goal of this dry etch process is to etch through the remaining silicon via the holes created using ZEP resist. The ZEP polymer is cleaned via resist stripping using oxygen plasma. After this process the device cross-section looks like Fig. 4.1 F.

#### **4.2.8 Wet etching and critical point drying**

The final step in the fabrication process consists of removing the HSQ and the underlying  $\text{SiO}_2$ . This is done via wet etching using HF for 200 seconds. The HF is diluted using cold water and then the chip is transferred to isopropanol ( $\text{CH}_3\text{CHOHCH}_3$ ). Drying MEMS in air or under vacuum can drastically alter their structures or even destroy them completely. A gentle method for such purposes is critical point drying. The surface tension of the water and isopropanol in a micro device is at the point at which a change from liquid to gaseous state can destroy the device through capillary forces. By increasing the pressure and temperature of the substrate it is possible to dry without crossing a phase boundary. This is possible because once the critical point has been passed, the density of liquid and gas are the same.  $\text{CO}_2$  is a good transitional fluid for which the critical point temperature and pressure are relatively low and hence the MEMS structures are not destroyed. After the critical point drying the device is developed with the structure as in Fig. 4.1 H.

### **4.3 Final product**

Show SEM image

# 5

Chapter 5

## Interpreting the results

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### 5.1 Experimental setup for measurement

### 5.2 Results

### 5.3 Analysis

# 6 Chapter 6

## Discussion

Add  
FOM

### 6.1 Limitations

### 6.2 Future work

# 7

## Chapter 7

# Conclusions

The demonstration of electrically controllable optical polarization rotation utilizing MEMS in silicon photonics establishes new horizons for on-chip integrated photonics. In addition to polarization rotators, dynamic control of optical polarization rotation can be utilized to realize a new class of components in integrated photonics including polarization mode modulators, multiplexers, filters, and switches for advanced optical signal processing, coherent communications, and sensing. Advanced sensors can be designed since more spectrometric analysis can be done using tunable modes. The TPR can also be used for developing integrated polarization stabilizer, PMD mitigation, PDL mitigation and PMD and PDL measurement systems. Also, since the power consumption of the TPR is very low, this can be used for reconfiguration of network topology at low power. Furthermore, if necessary, a cascade of MEMS TPR can be designed to yield broadband polarization rotation without the bandwidth constraints. Lastly, the measurement setup developed can be reused further to test future integrated photonics components using TE and TM modes.

# Appendix A: Abbreviations

**BPM** Beam propagation method. 10, 12

**CAGR** Compound annual growth rate. 4

**CMOS** Complementary metal-oxide semiconductor. 3, 4

**EM** Electromagnetic. 2, 6–8

**FDTD** Finite difference time domain. 10, 12

**FEM** Finite element method. 10, 12

**FIT** Finite integration technique. 10, 12, 13

**FOM** figures of merit. 18, 19

**HSQ** Hydrogen silsesquioxane. 50, 52–54

**IC** Integrated circuit(s). 3

**ICT** Information and communication technology. 2

**IL** Insertion loss. 19, 33

**IMS** IP Multimedia Subsystem. 2

**IoT** Internet of Things. 1

**MEMS** Microelectromechanical systems. 4, 5, 33, 40–42, 51, 54, 57

**NLC** Nematic liquid crystals. 32

**OEIC** Optoelectronic integrated circuit. 3, 4, 23, 24

**PBS** Polarization Beam Splitter. 44, 45, 47, 49–51

**PD $\lambda$**  polarization dependent wavelength characteristics. 4

**PDL** polarization dependent loss. 4, 21, 57

**PER** Polarization extinction ratio. 18, 25, 28–30, 33, 38, 49

**PMD** polarization mode dispersion. 4, 14, 21, 57

**PR** polarization rotator. 4, 6, 18, 23–31, 33, 34, 40, 41, 46, 50, 51

**RI** Refractive index. 8, 9, 11, 13, 16, 24, 31, 36, 37, 47, 48

**SMC** Single-mode condition. 10

**SOI** Silicon on Insulator. 51, 52

**SOP** state of polarization. 6, 16, 18, 30, 31

**TE** Transverse Electric. 9, 13–15, 17, 22–25, 28, 36, 39–41, 44, 45, 49–51

**TEM** Transverse Electromagnetic. 6, 8

**TM** Transverse Magnetic. 9, 14, 15, 22–25, 28, 36, 39–41, 44, 45, 49–51

**TPPS** Tunable polarization phase shifters. 29–31

**TPR** Tunable polarization rotator. 4, 5, 33, 42, 44–46, 57

**ZEP** ZEP7000. 50

# Appendix B: Graph generation script

```
1 %% Initialize variables.
2 filename = '/Users/Sandipan/Desktop/Test/mems.csv';
3 delimiter = ',';
4 startRow = 6;
5
6 %% Format string for each line of text:
7 % For more information, see the TEXTSCAN documentation.
8 formatSpec = '%f%f%q%f%[^\\n\\r]';
9 fileID = fopen(filename, 'r');
10
11 %% Read columns of data according to format string.
12 dataArray = textscan(fileID, formatSpec, 'Delimiter',
13     delimiter, 'EmptyValue', NaN, 'HeaderLines', startRow-1,
14     'ReturnOnError', false);
13 fclose(fileID);
14
15 %% Allocate imported array to column variable names
16 K=100;
17 w_RR = dataArray{:, 1};
18 w_slab = dataArray{:, 2};
19 %Slab width actual sizie scaling
20 w_slab = w_slab + 0.15;
21 w_RR(:) = round(w_RR(:)*K);
22 w_slab(:) = round(w_slab(:)*K);
23
24 lambda = abs(str2double(dataArray{:, 3}));
25 % Ratio of the polarization
26 rp = abs(real(log10(dataArray{:, 4})));
27 k = lambda>=1;
28 sums = accumarray( { w_RR(k), w_slab(k)}, rp(k), [], [], [],
29     true );
29 [i,j,k] = find(sums);
30
31 %% Draw area chart
32 figure
33 hold on
```

```

34 matrix = [i/K j/K k];
35 tri = delaunay(matrix(:,1),matrix(:,2));
36 trisurf(tri,matrix(:,1),matrix(:,2),matrix(:,3))
37 shading faceted
38 grid on
39 hold off
40
41 %%Draw 5 max on graph
42 hold on
43 N = 5;
44 [sortedX, sortedInds] = sort(k(:), 'ascend');
45 topN = sortedInds(1:N);
46 [m] = ind2sub(size(k), topN);
47
48 h = scatter3(i(m)/K,j(m)/K,k(m), 'filled', 'MarkerFaceColor',
    'red');
49 h.SizeData = 100;
50
51 text(i(m)/K,j(m)/K,k(m), strcat('(', num2str(i(m)/K), ',',
    num2str(j(m)/K), ')'), 'HorizontalAlignment', 'left', 'Color'
    , 'red', 'FontSize', 12)
52 hold off
53
54 %% Labels
55 xlabel('Rib width in \mu m', 'FontSize', 18, 'FontWeight', 'bold'
    , 'Color', 'black')
56 ylabel('Base width in \mu m', 'FontSize', 18, 'FontWeight', '
    bold', 'Color', 'black')
57
58 zlabel_eq = '$$\\sum_{mode}\\{abs\\left(log \\frac{E_{x_{mode}}}{E_{y_{mode}}}\\right)}$$';
59 zlabel(strcat('Log ratio of E-field = ', zlabel_eq), 'FontSize', 22, 'FontWeight', 'bold', 'Color', 'black', 'Interpreter', 'latex')
60
61 %% Clear temporary variables
62 clearvars filename delimiter startRow formatSpec fileID
    dataArray ans;

```

# **Todo list**

Less than copper...verify . . . . .	2
Add FOM . . . . .	56

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