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(54) **DELAY LOCKED LOOP CLOCK GENERATOR**

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(52) **U.S. Cl.** **327/158; 327/142**

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161; 377/47, 48

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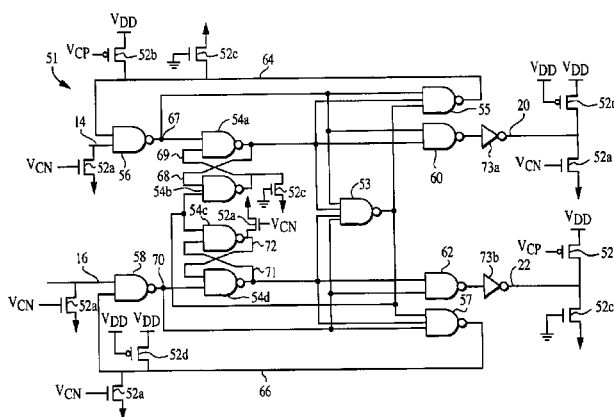
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ABSTRACT

A delay locked loop (DLL) clock generator circuit is provided for generating a clock signal Clk according to a pair of input signals to the circuit. One of the input signals is a reference signal, and the second input signal is a feedback signal of a voltage controlled delay line circuit. The DLL circuit includes a phase detector that can be reset to expand the locking range for detecting a phase difference between the reference signal and the feedback signal. Based on the detected phase difference, the phase detector provides an output signal that is further processed by the DLL circuit to generate a number of delayed signals to a frequency multiplier. Using the delayed signals, the frequency multiplier generates a frequency multiplied clock signal having a frequency that is a multiple of the frequency of the reference signal.

23 Claims, 5 Drawing Sheets



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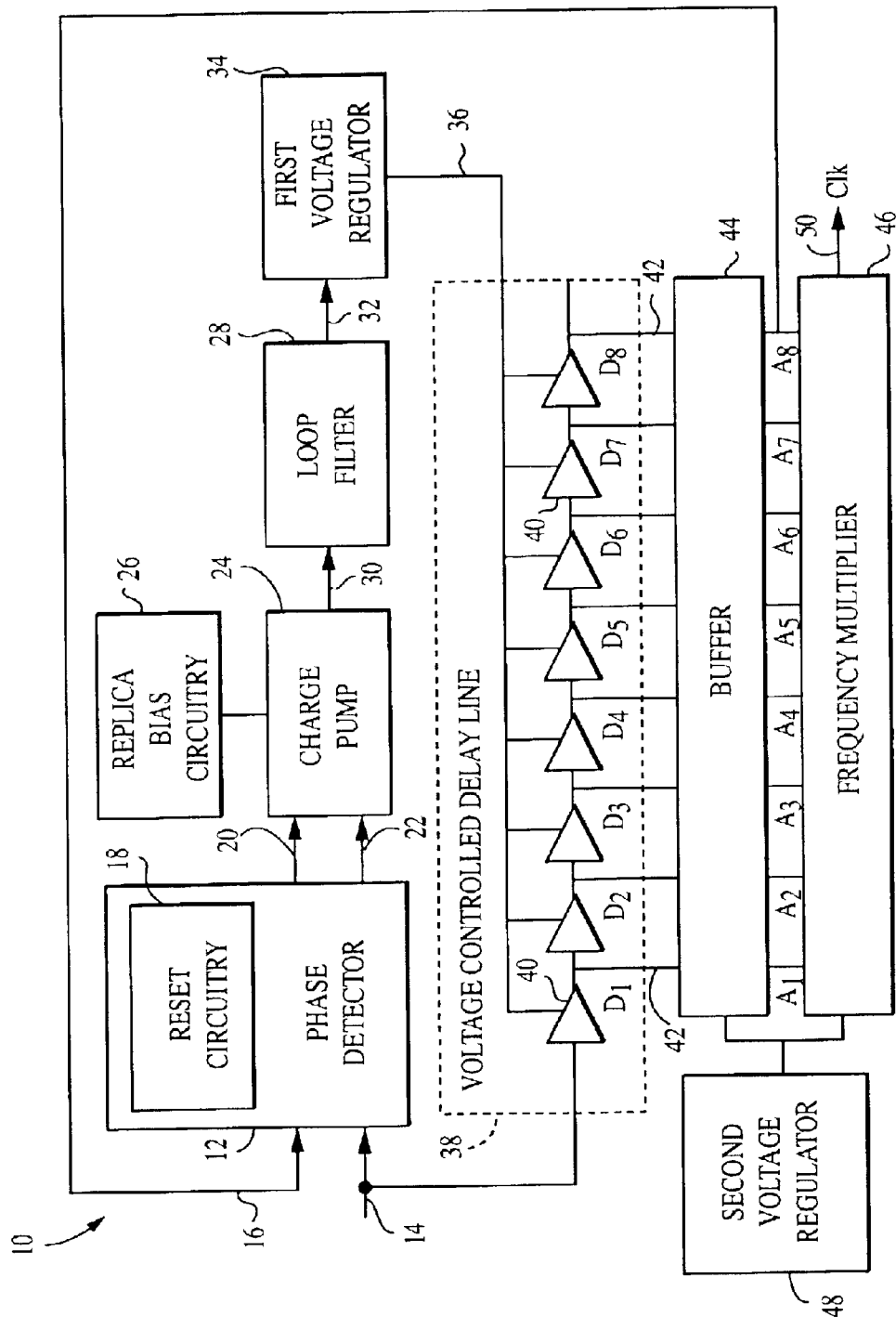


FIG. 1

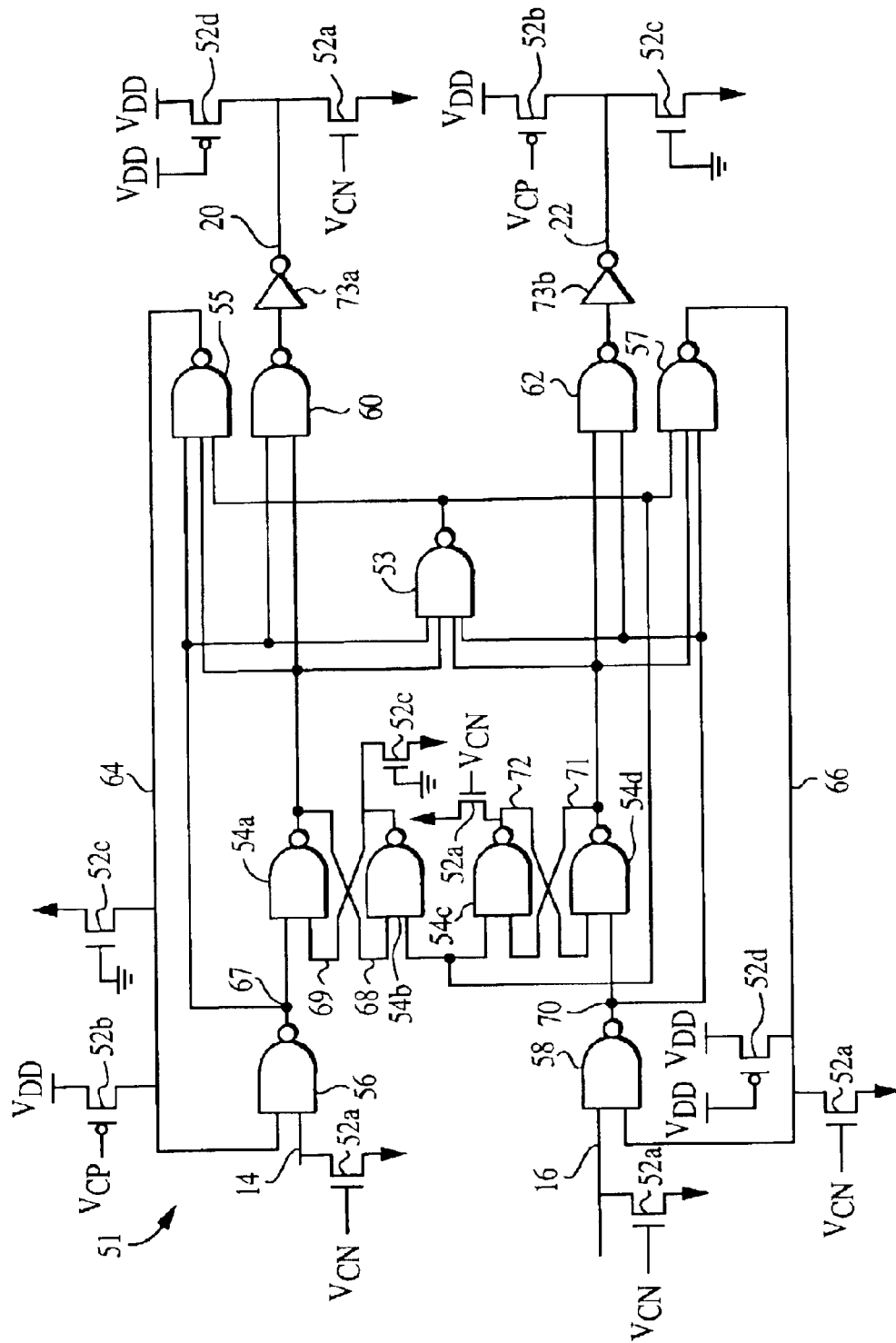
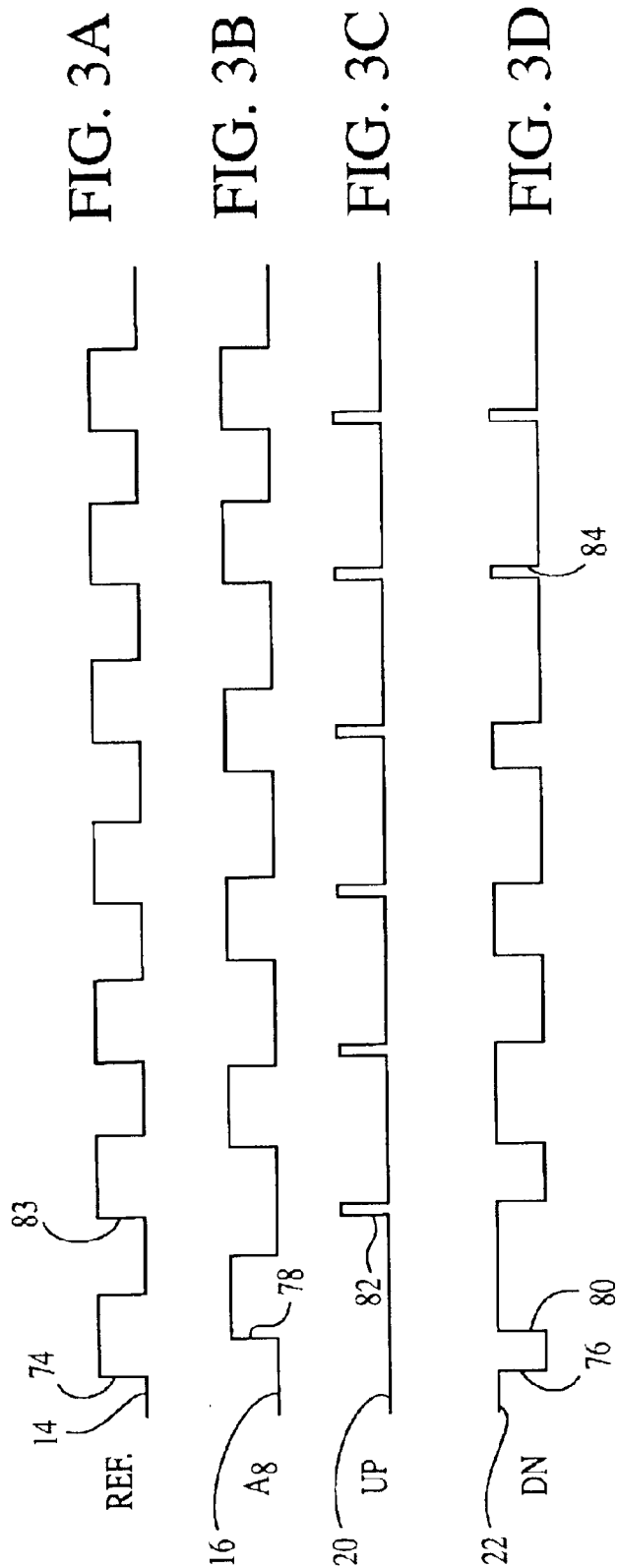


FIG. 2



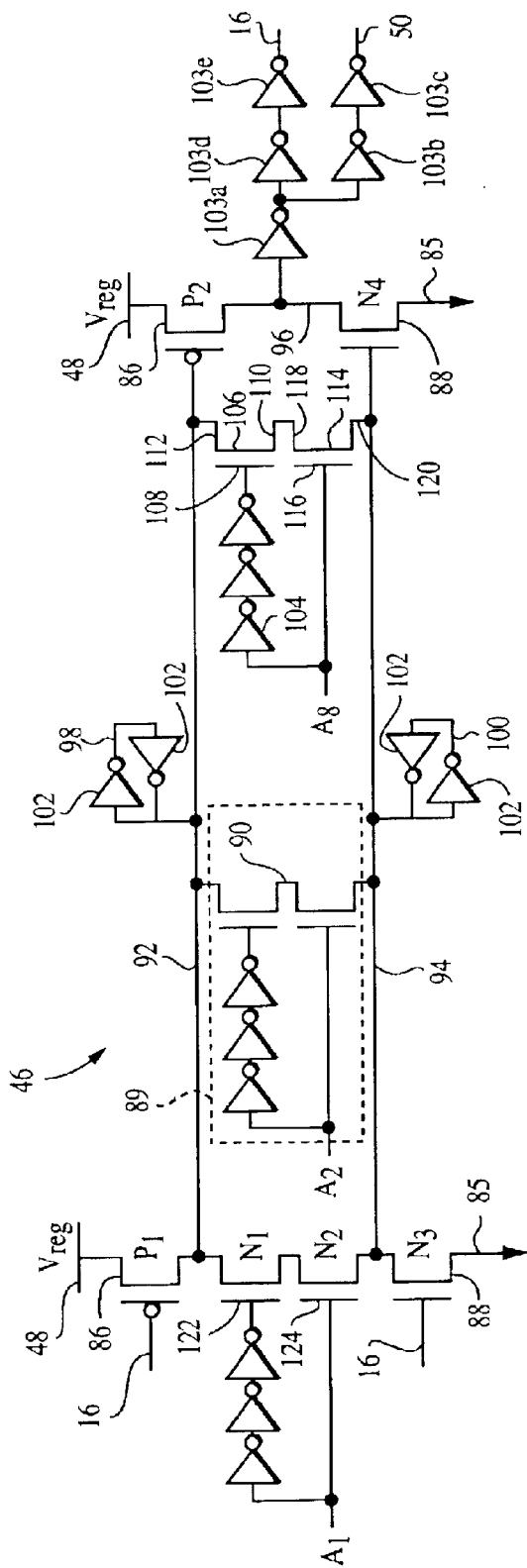


FIG. 4

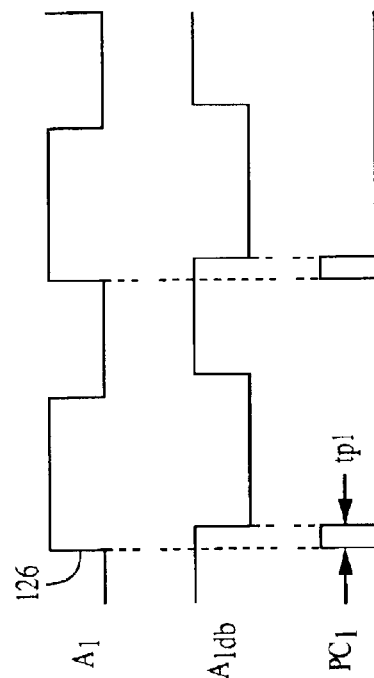
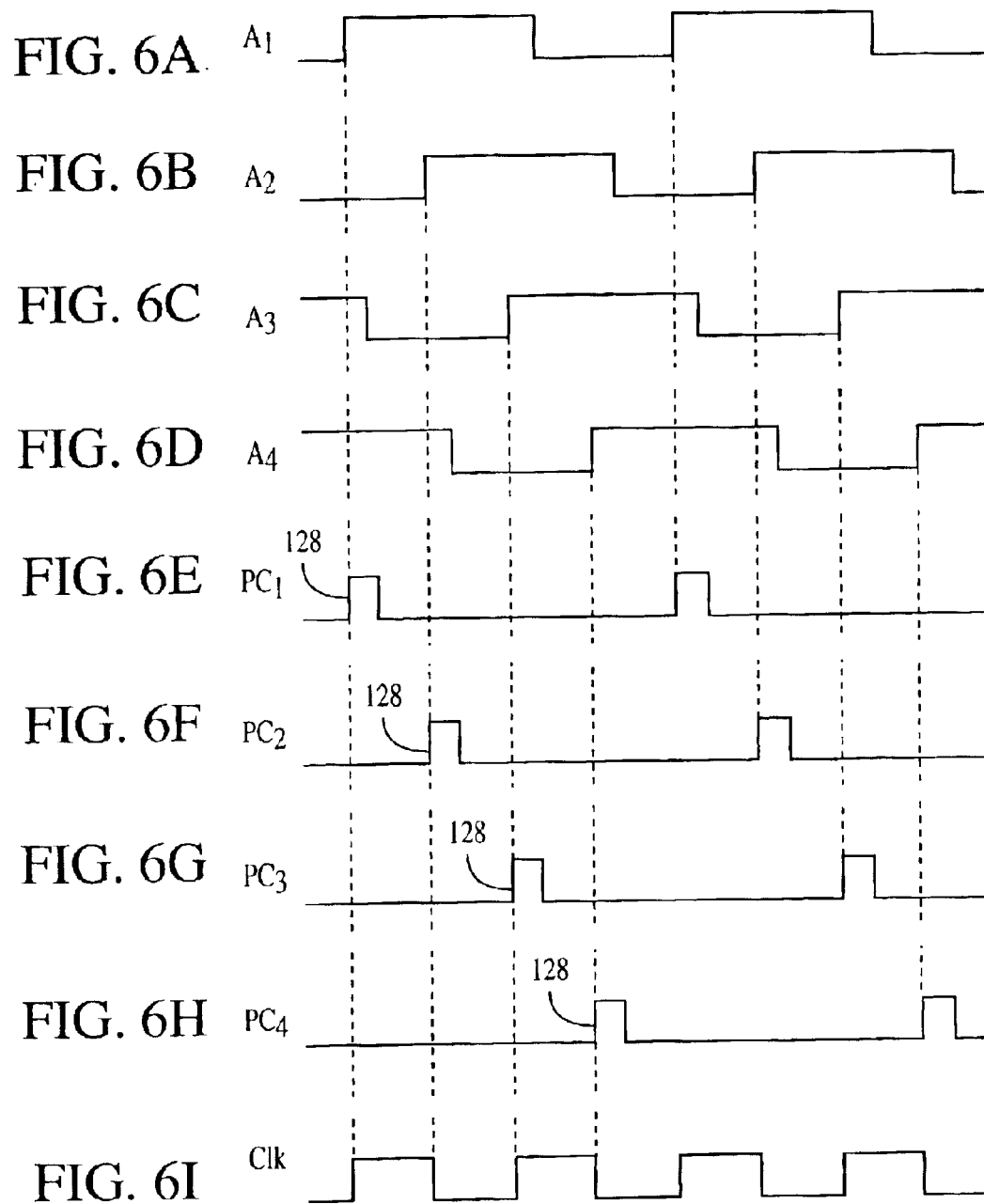


FIG. 5A

FIG. 5B

FIG. 5C



1

DELAY LOCKED LOOP CLOCK GENERATOR

FIELD OF THE INVENTION

The present invention relates to semiconductor electronic devices, and more particularly to clock generating circuits.

BACKGROUND OF THE INVENTION

Operation of a microprocessor, digital signal processor (DSP) and other integrated circuits, requires a system clock. Many clock generators in high-performance microprocessors employ a phase-locked loop (PLL) in their clock generation schemes to generate a clock signal. Generally, a PLL clock generator has a voltage-controlled oscillator (VCO), and a phase/frequency detector that receives an external reference input signal combined with a feedback input signal from the VCO. The PLL clock generator further includes a charge pump and a loop filter circuit connected in series between the phase/frequency detector and VCO. To generate the clock signal, a first divider circuit receives the VCO output and supplies the feedback input to the phase-frequency detector. A second divider circuit also receives the VCO output and generates the clock signal.

Another known clock generation scheme uses a delay locked loop (DLL). Generally, such systems have an external clock signal fed to a phase detector, a voltage controlled delay line (VCDL), and an input of an exclusive OR (XOR) gate that generates the frequency multiplied clock signal. In this clocking scheme, the phase detector outputs a signal to a loop filter which provides an output signal to the VCDL. The VCDL generates a first output that is fed to the XOR gate to generate a doubled frequency output.

PLL clock generators are known to have several disadvantages in comparison to DLL clock generators. First, a PLL clock generator is a higher-order circuit than a similar DLL clock generator circuit, and as such, is more difficult to design. Second, in a PLL clock generator the loop bandwidth critical for stable operation can change due to process, voltage and temperature variations. Moreover, the VCO output timing uncertainty or jitter accumulates over multiple oscillation cycles and is limited by the time response of the PLL clock generator. Furthermore, as new chip designs operate under increasingly noisy conditions and have delay variations due to power supply/substrate noises, existing PLL clock generators will not be able to provide instantaneous corrections to the delay variations.

DLL clock generators have several inherent advantages over PLL clock generators. DLL clock generators are first-order circuits which are more stable (i.e., have a stable loop operation), and are easily integrated with the loop filter. These advantages enable easier designs of DLL clock generators. Additionally, unlike PLL clock generators, DLL clock generators have no jitter accumulation. Moreover, DLL clock generators are fast locking. While DLL clock generators have advantages as compared to PLL clock generators, PLL generators are preferred for use in generating clock signals due to the difficulty of achieving frequency multiplication using a voltage-control delay line in DLL clock generators.

SUMMARY OF THE INVENTION

A delay locked loop (DLL) clock generator circuit is provided for multiplying a frequency of a reference signal inputted into the DLL circuit. The DLL circuit includes a

2

phase detector that receives the reference signal and a feedback signal of the DLL circuit to compare a phase difference or delay between the reference and feedback signals. Based on the phase difference, the phase detector provides a control voltage which is processed by the DLL circuit to generate a control signal. Preferably, the phase detector is reset by presetting gate voltages of the phased detector prior to receiving the feedback and reference signals. Resetting enables the phase detector to have an expanded locking range between the feedback and reference signals. The control signal is delayed at various time intervals to generate a number of delayed signals inputted into a frequency multiplier of the DLL circuit. Using the delayed signals, the frequency multiplier generates an output clock signal that has a frequency that is a multiple of the frequency of the reference signal.

BRIEF DESCRIPTION OF THE DRAWINGS

FIG. 1 illustrates a block diagram of a preferred embodiment for a DLL clock generator circuit;

FIG. 2 illustrates a circuit schematic of a phase detector having precharged nodes for the DLL clock generator of FIG. 1;

FIGS. 3A–3D are diagrams illustrating signal waveforms during the locking process of the phase detector of FIG. 1;

FIG. 4 illustrates a circuit schematic of a frequency multiplier for the DLL clock generator of FIG. 1;

FIGS. 5A–5C provide an illustration of the A_1 buffer input and the delayed $A_{1,b}$ buffer input which mimic a virtual pulse clock signal PC_1 , fed to the frequency multiplier of the DLL clock generator of FIG. 1; and

FIGS. 6A–6I are diagrams illustrating signal waveforms for one embodiment of a DLL circuit generating a clock pulse having a frequency multiplication of two.

DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

A delay locked loop (DLL) clock generator circuit is provided for generating a clock pulse based on a pair of input signals fed to the DLL circuit. One of the input signals is an external reference signal, and the other input signal is a time delayed feedback signal of a voltage controlled delay line circuit (VCDL). The DLL circuit includes a phase detector that detects a phase difference between the external reference signal and the feedback signal, and generates an output signal that is further processed by the DLL circuit to generate a number of delayed signals that are fed to a frequency multiplier. Using the delayed signals, the frequency multiplier generates a frequency multiplied clock signal based on the frequency of the reference signal.

FIG. 1 is a block diagram of a preferred embodiment DLL clock generator circuit 10. The DLL circuit 10 includes a phase detector 12 for detecting a phase difference between a reference signal 14 and a feedback signal 16. The phase detector 12 has reset circuitry 18 associated therewith to expand a locking range between the reference signal 14 and the feedback signal 16 for maintaining synchronization between the reference and feedback signals. In particular, the reset circuitry 18 is configured to charge or discharge one or more of a plurality of nodes (e.g., inputs and outputs of NAND gates) of the phase detector 12 to extend the phase delay locking range of the phase detector for aligning or synchronizing the delayed signals with the reference signal 14.

After receiving the reference signal 14 and feedback signal 16 inputs, the phase detector 12 generates phase

detector output signals that are outputted as either an up (UP) signal **20** or a down (DN) signal **22** according to the phase difference between the reference signal **14** and the feedback signal **16**. That is, the phase detector **12** produces output voltages that are proportional to the phase difference of the respective input reference signals **14** and feedback reference signals **16** concurrently inputted into the phase detector. Moreover, the UP signal **20** and/or the DN signal **22** can be transmitted from the phase detector **12** as a single signal or alternatively as multiple signals.

The UP signal **20** and/or DN signal **22** outputted from the phase detector **12** are inputted to a charge pump **24**. The charge pump **24** provides voltage signals responsive to the UP/DN signals **20**, **22** indicative of the phase difference between the phase detector input signals **14**, **16**. In addition to the phase detector **12**, a replica bias circuit **26** preferably connects to the charge pump **24** and enables the charge pump to operate accurately at high switching speeds. A loop filter **28** filters an output signal **30** from the charge pump **24** to reduce jitter in the output signal, and provides a loop filter output signal **32** to a voltage regulator **34**. The voltage regulator **34** further filters noise and jitter from the loop filter signal **32**, and provides a control signal **36** that is voltage regulated to a VCDL **38**. The reference signal **14** is also inputted into the VCDL **38**.

In a preferred embodiment for frequency multiplication by four, the VCDL **38** has a number of delay cells (D_1 – D_8) of serially connected inverter circuits **40** with a first delay cell D_1 receiving the reference signal **14**. For example, the DLL clock generator **10** can be implemented in a 0.35 micrometer single-poly four metal process with a 3.3V voltage supply. In addition, the charge pump **24** is preferably designed to avoid UP/DN current mismatches to achieve minimum static phase error over the maximum VCDL control voltage range, and the first voltage regulator **34** is designed with a single-pole regulating amplifier for regulating the supply voltage without compromising noise rejection and the overall loop bandwidth. The VCDL **38** has delay cells (D_1 – D_8) formed by inverter circuits **40** comprising two serially connected inverters. Delay of the VCDL **38** is accomplished by controlling the supply voltage provided by the voltage regulator **34** to the VCDL. The VCDL **38** provides delay cell output signals **42** from each of the inverter circuits **40** that are each phase delayed with respect to the control signals **36**. The delay cell output signals **42** are then fed into a level-shifting buffer **44** that provides output signals (A_1 – A_8) that are level-shifted to CMOS levels and fed into a frequency multiplier **46**. The buffer **44** additionally generates the feedback signal **16** to the phase detector **12** from the voltage controlled delay lines' final stage output (A_8). A second voltage regulator **48** connects and supplies power to the buffer **44** and the frequency multiplier **46** to minimize jitter of buffer output signals A_1 – A_8 , and a clock signal (Clk) **50** generated by the frequency multiplier. The frequency multiplier **46** generates Clk **50** in response to the rising edges of the buffer output signals (A_1 – A_8). That is, the Clk **50** is toggled for each rising edge of the buffer output signals (A_1 – A_8). An advantage of generating the Clk **50** in this manner is that even though the duty cycle ratio of the buffer output signals (A_1 – A_8) is not 50%, the Clk toggles at an even time interval.

The Clk **50** has a multiplied frequency relative to the input reference signal **14**, and can be used in various electronic devices such as a microprocessor, an audio or video appliance, memory, etc. By way of example, if the frequency of the reference signal **14** is 250 MHz, and the DLL circuit **10** is configured to have a frequency multiplication of four

(i.e., the VCDL **38** having eight delay cells), then the frequency of the Clk **50** is four times the reference signal frequency or 1 GHz. In other embodiments, the number of delay cells (D_1 – D_8) and outputs **42** from the VCDL **38** can be a number other than eight to provide a different frequency multiplication since the frequency of the Clk **50** is determined by multiplying the frequency of the reference signal **14** by the number of delay cells, and then dividing the result by two. The divide by two factor enables frequency multiplication that can be either an integer or a non-integer multiple of the reference signal frequency.

Referring now to FIG. 2, a preferred embodiment of the phase detector **12** and reset circuitry **18** are shown with a symmetrical circuit design structure **51** to minimize static phase error. In the preferred embodiment, an external reference signal **14** and a feedback signal **16** are inputted to the circuit **51**. In particular, the circuit **51** includes five NMOS transistors **52a** and two PMOS transistors **52b** to reset nodes. Additionally, the circuit **51** has three NMOS transistors **52c** and two PMOS transistors **52d** to minimize static phase offset. The circuit **51** also has a plurality of interconnected NAND gates that include an internal NAND gate **53**, a NAND gate pair **54a**, **54b**, a second NAND gate pair **54c**, **54d**, a feedback NAND gate **55**, and an input NAND gate **56**. The plurality of interconnected NAND gates further include a second feedback NAND gate **57**, a second input NAND gate **58**, and output NAND gates **60**, **62**.

A node **64** connects an input of gate **56** to an output of gate **55**, which provides a first internal feedback signal to gate **56**. The gate **56** also receives as an input the reference signal **14**. Similarly, a node **66** connects an input of gate **58** to an output of gate **57** which provides a second internal feedback signal to gate **58**. The gate **58** also receives the feedback signal **16** as an input. The NAND gate pair **54a** and **54b** are connected to an output **67** of gate **56**. A node **68** feeds, among other things, the output of gate **54a** to an input of gate **54b**. Another node **69** feeds the output gate **54b** to an input of gate **54a** enabling gates **54a** and **54b** to have outputs feeding each other. In a similar manner, gates **54c** and **54d** are connected to an output **70** of gate **58**. A node **71** feeds, among other things, the output of gate **54d** to an input of gate **54c**. Another node **72** feeds the output of gate **54c** to an input of gate **54d** enabling gates **54c** and **54d** to have outputs feeding each other. In addition to the plurality of interconnected NAND gates **54**, the circuit **51** further includes an inverter **73a** that generates as an output the UP signal **20**, and a second inverter **73b** that generates as an output the DN signal **22**.

In operation, the circuit **51** has nodes at the reference signal **14**, feedback signal **16**, the outputs of the inverters **73a**, **73b**, as well as internal nodes **64**, **66**, and **72** that are charged or discharged by their respective NMOS transistors **52a** or PMOS transistors **52b** to either a high voltage or a low voltage prior to the inputting of the reference signal **14** and the feedback signal **16** to the input NAND gates **56**, **58**. Preferably, the nodes for inputting the input reference signal **14** and feedback signal **16**, the output node **20** of the inverter **73a**, the node **66**, and the node **72** are discharged to a low voltage by the NMOS transistors **53a**. In addition, preferably the output node **22** of the inverter **73b** and the node **64** are charged to a high voltage by the PMOS transistors **53b**. High voltage and low voltage as discussed herein indicate a voltage level of nodes in the circuit. In one embodiment, a high voltage can be defined as VDD volts and a low voltage defined as zero volts. However, it is understood that alternative voltage selections defining the low and high voltages can be implemented as is known to those skilled in the art.

To discharge the nodes **14**, **16**, **20**, **66**, and **72**, a control signal V_{CN} is provided at respective gates of the NMOS transistors **52a**. Similarly, in order to charge the nodes **22**, **64**, a control signal V_{CP} is provided at respective gates of the PMOS transistors **52b**. The respective drains of the NMOS and PMOS transistors **52a** and **52b** are connected to the phase detector nodes that are charged or discharged. Moreover, in order to maintain symmetry in the circuit **51** and to reduce static phase offset, drains of the NMOS transistors **52c** are connected to nodes **22**, **64**, **69**, and their respective gates are preferably grounded. Also, the drains of PMOS transistors **52d** are connected to nodes **20**, **66**, and the respective gates of the transistors are preferably connected to a high voltage, such as V_{DD} .

FIGS. **3A–D** illustrate the locking process of the phase detector **12** of FIGS. **1** and **2** having charged or discharged nodes (i.e., inputs and/or outputs of one or more of the plurality of NAND gates of the phase detector and outputs **20**, **22** of the phase detector) prior to receiving a reference signal **14** and a feedback signal **16**. In order to have correct locking between the reference signal **14** and the delayed feedback signal **16** without charging or discharging of the phase detector's nodes, the delay of the delay line signal **16** should be in the following locking range:

$$T_{Ref}/2 < VCDL_{delay} < 3T_{Ref}/2, \quad (1)$$

where T_{Ref} and $VCDL_{delay}$ represent the period of the reference signal **14** and the delay of the delay line A_8 , respectively. That is, for correct locking $VCDL_{delay}$ should be equal to T_{Ref} . If the delay of the delay line A_8 deviates from the above locking range, the DLL clock generator **10** may be stuck or locked in an incorrect harmonic delay. Charging and discharging nodes of the phase detector **12** prior to the phase detector receiving the reference signal **14** and the feedback signal **16** changes the locking range of Eqn. 1. In particular, the locking range is expanded beyond the $T_{Ref}/2$ lower phase limit.

Referring again to FIGS. **3A–D**, the node of the DN output signal **22** is charged to a high voltage before the input reference signal **14** is inputted into the phase detector **12**. The rising edge **74** of a first pulse of the input reference signal **14** triggers the DN signal **22** to go to a low voltage state at **76**. The phase detector **12** can now compare the phase difference between the feedback signal (A_8) and the input reference signal **14** with the 2π phase offset once the phase of the feedback signal **16** is within a 3π range. This ensures that the lower boundary of limited locking range for the DLL clock generator **10** is eliminated enabling the VCDL output **42** to be initialized with a broader range. This broader range is advantageous as compared to other phase detectors whose locking range output for synchronization of the reference signal **14** and feedback signal **16** is narrower.

An example of the broader range locking range output is illustrated in FIGS. **3A–D**. When the feedback signal **16** goes to a high voltage **78**, the DN signal **22** goes to a high voltage **80**. Furthermore, when the UP signal **20** goes to a high voltage **82**, the input reference signal **14** goes to a high voltage **83**. Once the UP and DN signals **20**, **22** respectively are in a high voltage they remain at the high voltage for a short time and then return to a low voltage. The UP signal **20** increases the control voltage of the VCDL **38** and causes the VCDL outputs **42** to have smaller delays until the DLL clock generator circuit **10** is locked at pulse **84**. Once locked, the phase detector **12** generates only short pulses to prevent a dead zone of the phase detector. Further, the control voltage of the VCDL **38** is initialized to ensure that the VCDL delay is within the locking range, and can be initial-

ized within an expanded range due to the expanded locking range. That is, if the phase detector is reset by charging/discharging the phase detector's outputs and/or inputs to gates of the phase detector prior to receiving the reference signal **14** and the feedback signal **16**, then the locking range is expanded. Moreover, the phase difference has an upper limit only, and can be extended to a phase delay of 3π or less between the reference signal and the feedback signal.

FIG. **4** illustrates a circuit schematic of a preferred embodiment frequency multiplier **46** for the DLL clock generator circuit **10** of FIG. **1**. A regulated power supply signal, V_{reg} is provided by the second voltage regulator **48** to supply power for the frequency multiplier **46** which is connected to a low voltage, e.g., ground, at nodes **85**. The frequency multiplier **46** includes a plurality of PMOS transistors **86** (P_1 – P_2) and a plurality of NMOS transistors **88** (N_1 – N_4) matched and joined as a plurality of separate gate inputs configured to receive the buffer output signals (A_1 – A_8) of FIG. **1**. The feeding of the buffer output signals to the frequency multiplier **46** is illustrated by the subcircuit **89** receiving the A_2 buffer output signal. The A_2 buffer output signal is fed into cascaded transistor pairs, such as cascaded transistor pair **90**, which define frequency multiplier nodes **92**, **94**. The feeding of the A_1 and A_8 buffer output signals are also illustrated in FIG. **4**. In a similar manner to the subcircuit **89**, the A_3 – A_7 buffer output signals (not shown) are connected to the frequency multiplier nodes **92**, **94**.

The nodes **92**, **94** are charged to a high or low voltage according to the buffer output signals (A_1 – A_8). Preferably, a latch **98** connects to node **92** and a second latch **100** connects to node **94**. Each of the latches **98**, **100** includes a pair of inverters **102** connected in series. The frequency multiplier **46** is configured to generate two outputs. One output is the Clk **50** from the final stage output of inverters **103a**, **103b**, and **103c**, which are connected in series. The second output is the feedback signal **16** from the final stage output of inverters **103a**, **103d**, and **103e**, which are also connected in series.

In one embodiment, the plurality of separate gate inputs fed by the buffer outputs (A_1 – A_8) each comprise one or more gate input inverters **104** connected in series and configured to receive a single buffer output signal (e.g., A_8). The gate inputs further include a transistor **106** having a gate **108** connected to the one or more inverters **104**, a source **110**, and a drain **112** connected to the node **92**. Further included is a second transistor **114** that has a gate **116** configured to receive the final buffer output signal (A_8). The transistor **114** also has a drain **118** connected to the source **110** of transistor **106**, and a source **120** connected to node **94**. For the buffer output signal A_1 , a delayed version of the signal $A_{1,db}$ is fed to the gate **122** of the N_1 transistor, and the A_1 signal is fed to the gate **124** of the N_2 transistor to turn on and turn off the N_1 , and N_2 transistors, which charges and discharges the nodes **92**, **94** of FIG. **4**. More particularly, the A_1 and $A_{1,db}$ signals mimic generation of a virtual pulse clock signal PC_1 .

FIGS. **5A–C** provide an illustration of the virtual pulse clock signal PC_1 , due to the A_1 and $A_{1,db}$ inputs to the frequency multiplier **46**. In operation, when the feedback signal **16** is at a high voltage, the node **94** of the frequency multiplier **46** of FIG. **4** is discharged to a low voltage through NMOS transistor N_3 , and the node **92** remains at a high voltage. At a rising edge **126** of the A_1 signal, the delayed signal $A_{1,db}$ is at a high voltage and transistors N_1 , and N_2 are both turned on for a short time duration of $tp1$ and transfer data between the nodes **92** and **94**. If the node **92** is

7

discharged to a low voltage through transistors N_1 , N_2 , and N_3 after the A_1 signal rises to a high voltage, transistor P_2 charges output node 96 to a high voltage. After passing through the three serially connected inverters 103a, 103d, and 103e, the feedback signal 16 is at a low voltage and the node 92 is charged to a high voltage by transistor P_1 . The node 94 remains in a low voltage state. At a rising edge (not shown) of the A_2 signal inputted to the frequency multiplier 46, the data transfer from the node 92 to the node 94 occurs in a similar manner. After data transfer is completed, the node 94 drives transistor N_4 to discharge the node 96 to a low voltage resulting in the Clk 50 of FIG. 1 toggling between a high voltage and a low voltage at the rising edge of each delayed buffer output signal (A_1 – A_8).

FIGS. 6A–I provide an illustration of a generated clock pulse Clk using a frequency multiplier having four buffer output signals (A_1 – A_4) resulting in a frequency multiplication of two. In this illustration, the signals (A_1 – A_4) and associated delayed signals (A_{1db} – A_{4db}) (not shown) mimic four virtual pulse clock signals (PC_1 – PC_4). While the duty cycle ratio of the input signals (A_1 – A_4) is not 50%, the time intervals indicated by the rising edges 128 of the virtual pulse clock signals (PC_1 – PC_4) identify the even time interval toggling of the DLL generated clock signal Clk. Moreover, the frequency of the Clk can be controlled by the number of buffer output signals fed to the frequency multiplier as well as the frequency of the reference signal 14 inputted to the phase detector 12 of FIG. 1.

In a preferred embodiment, a method is provided for multiplying a frequency of a reference signal inputted into a delayed locked loop clock generator. The method includes the step of resetting a phase detector of the delayed locked loop clock generator to expand a locking range of the phase detector. Next, the method inputs the reference signal and a feedback signal to the reset phase detector to generate a control signal. The method also includes the steps of separating the control signal into one or more delayed signals, and then generating a clock signal toggled at an edge of each of the one or more delayed signals. At least one of the one or more delayed signals can be the feedback signal, and is preferably the final stage delayed signal.

Preferably, the expansion of the locking range allows a 3π phase delay between the reference signal and the feedback signal with an upper phase delay limit of 3π . In other expanding locking range schemes, the locking range includes an unlimited lower phase limit. Expansion of the locking range occurs due to resetting of the phase detector. Resetting occurs by charging or discharging inputs to gates of the phase detector, and also in one embodiment outputs of the phase detector. In other embodiments, the control signal can be filtered prior to separating the control signal, and/or the one or more delay signals can be buffered prior to generating the clock signal.

While specific embodiments of the present invention have been shown and described, it should be understood that other modifications, substitutions and alternatives are apparent to one of ordinary skill in the art. Such modifications, substitutions and alternatives can be made without departing from the spirit and scope of the invention, which should be determined from the appended claims.

Various features of the invention are set forth in the appended claims.

What is claimed is:

1. A method for multiplying a frequency of a reference signal inputted into a delayed locked loop clock generator, the method comprising the steps of:

resetting a phase detector of the delayed locked loop clock generator by presetting at least one output gate voltage

8

of an output gate of the phase detector to enable a feedback signal to be inputted into the phase detector with a phase delay relative to the reference signal and remain synchronized with the reference signal;

generating a control signal in response to the phase delay; separating the control signal into one or more delayed signals; and

generating a clock signal toggled at an edge of each of the one or more delayed signals.

2. The method of claim 1, wherein the phase delay is 3π or less between the reference signal and the feedback signal.

3. The method of claim 1, wherein the phase delay between the reference signal and the feedback signal has an upper phase delay limit of 3π and a lower phase delay limit less than 3π .

4. The method of claim 3, wherein the lower phase delay limit between the reference signal and the feedback signal is eliminated.

5. The method of claim 1, wherein resetting of the phase detector includes the step of one of charging and discharging inputs to NAND gates of the phase detector.

6. The method of claim 5, wherein resetting of the phase detector further includes the step of one of charging and discharging outputs of the phase detector.

7. The method of claim 1, further comprising the step of buffering the one or more delayed signals prior to generating the clock signal.

8. The method of claim 1, further comprising the step of filtering the control signal prior to separating the control signal.

9. The method of claim 8, wherein the feedback signal comprises one of the one or more delayed signals.

10. The method of claim 1, wherein the one or more delayed signals have a duty cycle ratio other than 50%.

11. A delayed locked loop clock generator circuit comprising:

a voltage controlled delay line receiving as an input a reference signal;

a frequency multiplier receiving delayed output signals from the voltage controlled delay line to generate a clock signal having a multiplied frequency relative to a frequency of the reference signal; and

a phase detector having a plurality of output gates and receiving the reference signal and a delayed feedback signal to produce a control signal proportional to a phase delay of 3π or less between the delayed feedback signal of the voltage controlled delay line and the reference signal, the control signal provided as a controlled voltage to the voltage controlled delay line, and wherein the phase detector is reset by presetting at least one output gate voltage of the output gates.

12. The delayed locked loop clock generator of claim 11, wherein the phase delay between the delayed feedback signal and the reference signal has an upper phase delay limit only.

13. The delayed locked loop clock generator of claim 12, wherein one of the delayed output signals is the delayed feedback signal.

14. The delayed locked loop clock generator of claim 13, wherein the phase detector is reset prior to receiving the reference signal and the delayed feedback signal.

15. The delayed locked loop clock generator of claim 14, wherein resetting of the phase detector comprises one of charging and discharging inputs to gates of the phase detector.

16. The delayed locked loop clock generator of claim 15, wherein the resetting of the phase detector further comprises one of charging and discharging outputs of the phase detector.

9

17. The delay locked loop clock generator of claim 11, wherein the frequency multiplier toggles the frequency multiplied clock signal between one of a low voltage and a high voltage for each rising edge of the delayed output signals of the voltage controlled delay line.

18. The delayed locked loop clock generator circuit of claim 11, wherein the delayed output signals have a duty cycle ratio other than 50%.

19. A delayed locked loop clock generator comprising:

a voltage controlled delay line receiving a control signal to generate a plurality of delayed output signals;

a phase detector having at least one output of an output gates reset prior to accepting a feedback signal from the voltage controlled delay line and a reference signal, the phase detector producing the control signal according to a phase delay between the feedback signal and the reference signal; and

a frequency multiplier responsive to the reference signal and an edge of each of the plurality of delayed output

10

signals, the frequency multiplier generating a clock signal toggled between the low voltage and the high voltage at each edge of the plurality of delayed output signals.

20. The delayed locked loop clock generator of claim 19, wherein the phase delay is 3π or less between the reference signal and the feedback signal.

21. The delayed locked loop clock generator of claim 20, wherein the phase detector has one or more of a plurality of NAND gates having inputs and outputs that are one of charged and discharged prior to the phase detector receiving the reference signal and the feedback signal.

22. The delayed locked loop clock generator of claim 19, wherein a rising edge of each of the plurality of delayed output signals toggles the clock signal.

23. The delayed locked loop clock generator of claim 19, wherein the plurality of delayed output signals have a duty cycle ratio other than 50%.

* * * * *

UNITED STATES PATENT AND TRADEMARK OFFICE
CERTIFICATE OF CORRECTION

PATENT NO. : 6,784,707 B2
DATED : August 31, 2004
INVENTOR(S) : Kim et al.

Page 1 of 1

It is certified that error appears in the above-identified patent and that said Letters Patent is hereby corrected as shown below:

Column 5,

Line 4, delete "VCP" and insert -- Vcp -- therefore

Column 6,

Line 47, delete "1 16" and insert -- 116 -- therefore

Column 8,

Line 51, after "claim 11" insert -- wherein -- therefore

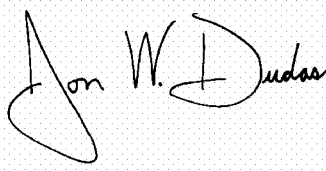
Line 54, delete "12" and insert -- 11 -- therefore

Column 9,

Line 13, delete "gate" and insert -- gates -- therefore

Signed and Sealed this

Fifth Day of April, 2005

A handwritten signature in black ink, reading "Jon W. Dudas". The signature is written in a cursive style with a large, stylized "J" and "D".

JON W. DUDAS

Director of the United States Patent and Trademark Office