Channel Shaping Using Reconfigurable Intelligent Surfaces: From Diagonal to Beyond

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I. Assumption

All proposals in this paper based on assumption of *asymmetric* passive Beyond-Diagonal (BD) Reconfigurable Intelligent Surface (RIS), i.e., symmetry constraint $\mathbf{\Theta}_g = \mathbf{\Theta}_g^{\mathsf{T}}$ is relaxed. This is feasible when asymmetric passive components (e.g., ring hybrids and branch-line hybrids) [1] are available. This assumption was also made in Hongyu's papers [2], [3]. For quadratic problems, the proposed algorithms may be extended to symmetric BD RIS by replacing singular value decomposition with Takagi factorization [4].

II. Point-to-Point MIMO

A. Channel Power Maximization

Consider a BD RIS with N_{S} elements, which is divided into G groups of equal L elements.

$$\max_{\mathbf{\Theta}} \quad \left\| \mathbf{H}^{\mathrm{D}} + \sum\nolimits_g \mathbf{H}_g^{\mathrm{B}} \mathbf{\Theta}_g \mathbf{H}_g^{\mathrm{F}} \right\|_{\mathrm{F}}^2 \tag{1a}$$

$$\text{s.t.} \quad \mathbf{\Theta}_g^{\mathsf{H}} \mathbf{\Theta}_g = \mathbf{I}_L, \quad \forall g \in \mathcal{G} \triangleq \{1,\ldots,G\} \tag{1b}$$

For *symmetric* BD-RIS, the problem has been solved in

- Matteo's paper [5]: SISO and equivalent[1];
- Ignacio's paper [6]: SISO and directless MISO/SIMO.

Remark 1. *The difficulty of* (1) *is that the RIS needs to balance the additive (direct-indirect) and multiplicative (forward-backward) eigenspace alignment. Interestingly, it has the same form as the* weighted orthogonal Procrustes problem *[7]:*

$$\min_{\mathbf{\Theta}} \quad \|\mathbf{C} - \mathbf{A}\mathbf{\Theta}\mathbf{B}\|_F^2 \tag{2a}$$

$$\text{s.t.} \quad \mathbf{\Theta}^{\mathsf{H}}\mathbf{\Theta} = \mathbf{I} \tag{2b}$$

There exists no trivial solution to (2). *One lossy transformation, by moving* $\mathbf{\Theta}$ *to one side [8], formulates a standard orthogonal Procrustes problem:*

$$\min_{\mathbf{\Theta}} \quad \|\mathbf{A}^{\dagger}\mathbf{C} - \mathbf{\Theta}\mathbf{B}\|_F^2 \tag{3a}$$

$$\text{s.t.} \quad \mathbf{\Theta}^{\mathsf{H}}\mathbf{\Theta} = \mathbf{I} \tag{3b}$$

(3) *has a global optimal solution* $\mathbf{\Theta}^{\star} = \mathbf{U}\mathbf{V}^{\mathsf{H}}$, *where* $\mathbf{U}$ *and* $\mathbf{V}$ *are left and right singular matrix of* $\mathbf{A}^{\dagger}\mathbf{C}\mathbf{B}^{\mathsf{H}}$ *[9]. This low-complexity solution will be compared with the one proposed later.*

Inspired by [10], we propose an iterative algorithm to solve (1). The idea is to successively approximate the quadratic objective with a sequence of affine functions and solve the resulting subproblems in closed form.

[1] Single-stream MIMO with given precoder and combiner.

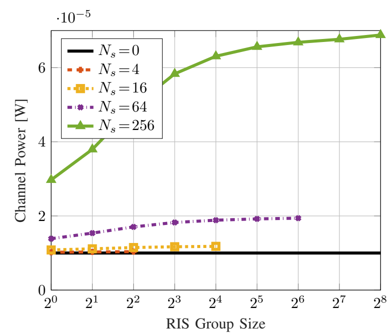
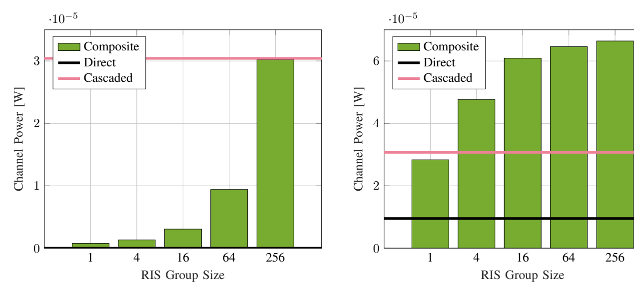


Fig. 1. Average channel power versus RIS elements N_{S} and group size L for $(N_{\mathrm{T}}, N_{\mathrm{R}}) = (8,4)$, $(\Lambda^{\mathrm{D}}, \Lambda^{\mathrm{F}}, \Lambda^{\mathrm{B}}) = (65,54,46)$dB.



(a) Without Direct Link

(b) With Direct Link

Fig. 2. Average channel power versus RIS group size L for $(N_{\mathrm{T}}, N_{\mathrm{S}}, N_{\mathrm{R}}) = (8,256,4)$, $(\Lambda^{\mathrm{D}}, \Lambda^{\mathrm{F}}, \Lambda^{\mathrm{B}}) = (65,54,46)$dB.

Proposition 1. *Start from any* $\mathbf{\Theta}^{(0)}$, *the sequence*

$$\mathbf{\Theta}_g^{(r+1)} = \mathbf{U}_g^{(r)} \mathbf{V}_g^{(r)}, \quad \forall g \in \mathcal{G} \tag{4}$$

converges to a stationary point of (1), *where* $\mathbf{U}_g^{(r)}$ *and* $\mathbf{V}_g^{(r)}$ *are left and right singular matrix of*

$$\begin{aligned} \mathbf{M}_g^{(r)} = {} & \mathbf{H}_g^{\mathrm{B}\,\mathsf{H}} \mathbf{H}^{\mathrm{D}} \mathbf{H}_g^{\mathrm{F}\,\mathsf{H}} + \sum_{g' < g} \mathbf{H}_{g'}^{\mathrm{B}\,\mathsf{H}} \mathbf{H}_{g'}^{\mathrm{B}} \mathbf{\Theta}_{g'}^{(r+1)} \mathbf{H}_{g'}^{\mathrm{F}} \mathbf{H}_{g'}^{\mathrm{F}\,\mathsf{H}} \\ & + \sum_{g' \geq g} \mathbf{H}_{g'}^{\mathrm{B}\,\mathsf{H}} \mathbf{H}_{g'}^{\mathrm{B}} \mathbf{\Theta}_{g'}^{(r)} \mathbf{H}_{g'}^{\mathrm{F}} \mathbf{H}_{g'}^{\mathrm{F}\,\mathsf{H}}. \end{aligned} \tag{5}$$

Proof. To be added. □

Fig. 1 shows that, apart from adding reflecting elements N_{S}, increasing the group size L also improves the channel power. This behavior is more pronounced for a large RIS. For example, the gain of pairwise connection is 2.8% for $N_{\mathrm{S}} = 16$

and 28% for $N_{\mathrm{S}}=256$. It implies that the channel shaping capability of BD RIS scales with group size L.

Fig. 2b and 2a compare the average channel power without and with direct link. “Cascaded” means the *power product* of the forward and backward channels. We observe that diagonal RIS wastes substantial cascaded power and struggles to align the direct-indirect eigenspace. When the direct link is absent, only 2.6% of available power is utilized by diagonal RIS while 100% power is recycled by fully-connected RIS. When the direct link is present, the proposed BD RIS design can balance the direct-indirect and forward-backward eigenspace alignment for an optimal channel boost. It is worth noting that, when L is sufficiently large, the composite channel power surpasses the power sum of direct and cascaded channels, thanks to the constructive *amplitude superposition* of direct and cascaded channels. This again emphasizes the advantage of in-group connection of BD RIS.

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