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Sensor Fusion for Irregularly Sampled Systems

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List of Symbols and Acronyms

Symbols

Chapter 1

\mathbb{N}^+	positive integers;
\mathbb{R}	real numbers;
\mathbb{R}^n	$\mathbb{R}^{n \times 1}$ n -dimensional Euclidean space;
\forall	for all;
\in	belongs to;
$>$	greater than;
$<$	less than;
\geq	greater than or equal to;
\leq	less than or equal to;
\triangleq	equals by definition;
\approx	approximately equal to;
\sim	is distributed as;
$\mathcal{E}(\lambda)$	exponential distribution with rate parameter λ ;
$E[\cdot]$	mathematical expectation;
x_i	i th entry of \mathbf{x} ;
f	process model;
g	observation model;
t	continuous-time index;
k	discrete-time index of measurements;
i	discrete-time index of input;
t_k	continuous-time sampled instants;

T	input sampling interval;
$x(t)$	state vector;
$\dot{x}(t)$	derivative of the state vector with respect to t ;
$x(t_k)$	state vector at continuous-time sampled instants;
$u(t)$	input vector;
$u(iT)$	input vector at continuous-time sampled at time $t = iT$;
$w(t)$	process noise vector;
$y(t_k)$	output vector at continuous-time sampled instants;
δ_k	measurements time-delay;
$v(t_k)$	measurement noise vector;
h_k	time intervals between two continuous-time sampled instants;
λ	parameter of the exponential distribution;
λ_h	parameter of the exponentially distributed random variable h_k ;
λ_{δ_k}	parameter of the exponentially distributed random variable δ_k ;
N	amount of identical sensors in the sampling model;
L	sampling period of the identical sensors in the sampling model;
P	covariance matrix;
α	relation between output (expected) and input sampling time intervals .

Chapter 2

$\mathcal{N}(\mu, \sigma)$	Gaussian distribution with mean μ and standard deviation σ ;
\mathbb{P}	power set;
μ	mean of a random variable;
σ	standard deviation of a random variable;
n	number of homogeneous sensors;
E	evidence;
H	hypothesis;
R_i	i^{th} fuzzy rule;
x_k	k^{th} input fuzzy variable;
$A_{i,j}$	j^{th} antecedent fuzzy set for the i^{th} rule;
y_i	i^{th} consequent output variable for the i^{th} rule;
C_i	consequent class for the i^{th} rule;
X	input vector;

A	fuzzy set;
U	universe of discourse;
B	subset of features;
$B_*(X)$	B -lower approximation of X ;
$B^*(X)$	B -upper approximation of X ;
$BN_B(X)$	B -boundary region of X ;
$\rho(x)$	probability density function of x ;
$\rho(H E)$	conditional probability density function of H given E ;
$\pi_x(u)$	possibility distribution of x associated with u ;
$\mu_A(x)$	membership function of x of a fuzzy set A ;
\subseteq	is a subset of;
\cap	set intersection;
\emptyset	empty set;

Chapter 3

\mathbb{N}	natural numbers;
\mathbb{R}	real numbers;
\mathbb{R}^n	$\mathbb{R}^{n \times 1}$ n -dimensional Euclidean space;
$Ber(p)$	Bernoulli distribution with parameter p ;
$\mathcal{N}(\mu, \sigma)$	Gaussian distribution with mean μ and standard deviation σ ;
$\Gamma(\kappa, \theta)$	gamma distribution with shape parameter κ and scale parameter θ ;
$E[\cdot]$	mathematical expectation;
$Var[\cdot]$	variance;
\forall	for all;
$>$	greater than;
\geq	greater than or equal to;
\sim	is distributed as;
\pm	plus or minus;
y_t, y_k, y_{kT}	output vector at continuous-time sampled instants;
$z(t)$	measurement output;
$H(k), L(k), C, D$	matrices of the observation model;
$v(t), v(k)$	measurement noise vector;
t_i, t_k	continuous-time sampled index;

k	discrete-time index of measurements;
T	expected sampling time interval;
$d(k)$	observation sampling time delays;
l	amount of different known delays;
$\xi(t)$	Bernoulli random variable that models packet dropout and uncertain observation;
$C_i(t)$	real time approximation from the i^{th} computer clock;
a_i	i^{th} clock drift;
b_i	i^{th} clock offset;
a_{ij}	relative drift between i^{th} and j^{th} node;
b_{ij}	relative offset between i^{th} and j^{th} node;
Δ	measured value interval between observations;
δ_k	random time interval;
$p(k)$	Bernoulli distribution parameter;
ϵ_k	deviation from expected time instants;
σ	standard deviation;
κ	shape parameter;
θ	scale parameter;
μs	micro seconds;
$E.E$	energy efficiency;
$Comp.$	complexity;

Chapter 4

\mathbb{R}^n	$\mathbb{R}^{n \times 1}$ n -dimensional Euclidean space;
$\mathcal{N}(\mu, \sigma)$	Gaussian distribution with mean μ and standard deviation σ ;
$E[\cdot]$	mathematical expectation;
\triangleq	equals by definition;
$\arg \max_x f(x)$	argument x that maximizes function $f(x)$;
$\rho(x y)$	conditional probability density function of X given Y ;
x_k	state vector;
\hat{x}_k	estimated state vector;
y_k	observation vector;
σ	standard deviation;
Σ	covariance matrix;

Chapter 5

Acronyms

CDF	Cumulative Distribution Function;
CU	Covariance Union;
DAI	Data In;
DAO	Data Out;
DEI	Decision In;
DEO	Decision Out;
DMTS	Delay Measurement Time Synchronization;
DSET	Dempster-Shafer Evidence Theory;
EKF	Extended Kalman Filter;
FEI	Feature In;
FEO	Feature Out;
FIS	Fuzzy Inference System;
FISST	Finite-Set Statistics;
FTSP	Flooding Time Synchronization Protocol;
GPS	Global Positioning System;
HMM	Hidden Markov Model;
KF	Kalman Filter;
UKF	Unscented Kalman Filter;
LEETS	Lightweight and Energy Efficient Time Synchronization;
LTS	Lightweight Tree-based Synchronization;
LTI	Linear Time-Invariant;
LS	Least Squares;
MAP	Maximum A Posteriori;
ML	Maximum Likelihood;
MMSE	Minimum Mean Square Error;
MOP	Measures Of Performance;
NEES	Normalized Estimation Error Squared;
NIS	Normalized Innovation Squared;
NMR	Nuclear Magnetic Resonance;
NTP	Network Time Protocol;
NUS	Non-Uniform Sampling;
OOSM	Out-Of-Sequence Measurement;

PDF	Probability Density Function;
PDAF	Probabilistic Data Association Filter;
PF	Particle Filter;
PRBS	Pseud-Random Binary Sequence;
RBS	Reference Broadcast Synchronization;
RMSE	Root Mean Square Error;
RTPF	Real-Time Particle Filter;
RV	Random Variable;
SOD	Send-On-Delta;
SNR	Signal-to-Noise Ratio;
TDS	Time-Delay System;
TDP	Time-Diffusion Protocol;
TPSN	Timing-sync Protocol for Sensor Networks;
TSST	Time Synchronization based on Spanning Tree;
TTF	Track-to-Track Fusion;
UKF	Unscented Kalman Filter;
WSN	Wireless Sensor Networks;
ZOH	Zero-Order Holder;

Introduction

1.1 Motivation

In nature it is possible to observe data fusion in a variety of phenomena. Animals combine signals from different senses, such as sight, hearing, smell, taste and touch, to recognize the surroundings. Plants have analogous mechanisms, which are used to modulate water consumption, to change the color of their leaves or to bend their structures towards the light, for instance. Throughout history, the sensory systems in living beings have evolved to assimilate multiple information coming from numerous sources in a highly complex and efficient way, in order to have a better perception of the environment.

Nowadays information fusion is studied in many fields of science, as a way of exploiting data from multiple sources to achieve better outcomes in comparison to those obtained if any of the sources were used separately (Dasarathy, 2001). Other terms have been used to denote the synthesis of information in technical literature, for instance, data fusion, sensor fusion, combination of evidence and synthesis of observations (Goodman et al., 1997). To avoid confusion, the terminology used by (Elmenreich, 2002) will be adopted, whereby information fusion is understood as the overall term and sensor fusion is used in cases for which the sources of information are sensors.

Some research fields have been increasingly exploiting the advantages of sensor fusion techniques, such as robotics, military, biometrics and image processing. The main benefits expected are related to accuracy, due to the use of redundant or complementary data; to dimensionality, that is additional information being created by a group of data; and to robustness against failures and interference. Consequently much effort has been put into the development and investigation of data fusion techniques. The work of (Khaleghi et al., 2013) presents an extensive review of different approaches available, categorizing them by the way sensor data imperfection is represented, namely, proba-

bilistic fusion, evidential belief reasoning, fuzzy reasoning, possibilistic fusion, rough set-based fusion, random set-based fusion and hybrid fusion.

Data fusion techniques based on probability theory are the earliest available and perhaps the most popular until now. They are concerned with estimating the probability density functions (PDFs) of the system states by means of the Bayesian approach. If the system is linear and Gaussian, then the Kalman filter (KF) guarantees optimal estimation. For nonlinear processes, KF generalizations were proposed, such as the extended Kalman filter (EKF) or the unscented Kalman filter (UKF) (Julier and Uhlmann, 2004). On the other hand, particle filters (PF) can be used to deal with both nonlinearities in the dynamics and non-Gaussian distributions (Arulampalam et al., 2002).

The most common class of systems studied in state estimation is the class of sampled-data systems, due to the wide use of digital devices. Although often described by continuous time differential equations, they can be modeled using discrete state equations, using approximation techniques (Phillips and Nagle, 1995). Usually the sampling period of such systems are constant and known. In other words, the sensors are considered to transmit data at regular intervals. However, for many applications, such assumption is not valid. The use of several redundant sensors, for example, with different sampling rates or unsynchronized with one another, leads to data being received at irregular instants. Additionally, when data from multiple sensors are transmitted through several subsystems in a network, there might be loss of packets and delays (Schenato et al., 2007) or even multiple information arriving simultaneously (Moayedi et al., 2011). In networked control systems, event-triggered sampling schemes have been proposed to optimize the access to communication channels (Hu et al., 2017), which will also generate time-varying sampling intervals. Nowadays, because of the ever-growing scientific advances, the technology of microprocessors, sensors and communication has become increasingly accessible, which continues to ensure that multiple sensor networks are more and more common.

Thus, despite improving accuracy and robustness of the estimation process, the fusion of data from multiple sensors might introduce challenges to the state estimation algorithms, due to sampling irregularities. Depending on how they take place, modifications to the KF and its generalizations can be carried out to tackle these abnormalities. In the work of (Fatehi and Huang, 2017), a fusion KF is proposed to estimate the states of a system with multi-rate measurements, whereby one of them is fast, regular and delay-free and the other is slow, irregular and randomly delayed. One application

of such system is for industrial process control, where there is online instrumentation characterized by the former and data from laboratory analysis, which are much more accurate. For a more general case, when the random delays are unknown, the work of (Gopalakrishnan et al., 2010) presents a critical analysis of the available methods for data fusion. They are separated into two categories: those that incorporate the delayed measurements upon arrival, and methods that rely on state augmentation, in order to assimilate the delayed information between estimation steps.

In general the proposed methods and their performance will depend on the characteristics of the sampling irregularities and how they are modeled. Time delays can be multiples of a base sampling period, for instance. In those cases, delays can happen at single or multiple lags (Peñarrocha et al., 2012), can lead to out-of-sequence measurements (Anxi et al., 2005; Westenberger et al., 2013) or there can also be data dropout (Zhu et al., 2013). Nevertheless, the system can be described by a time-invariant discrete state equation, with particular representations of the observation model. When measurement are taken after random time intervals, the discrete-state representation leads to a time-varying system, since the sampling period changes over time. Some researchers treat the variable measurement instants as stochastic processes (Micheli and Jordan, 2002) or as a periodic sampling interval subject to noisy perturbations (Shen et al., 2016). Generally, the instant is considered to be known and the methods assimilate such information in the algorithm, that is the random time intervals are considered as measurements themselves.

To the best of the author's knowledge, no method was proposed so far, for cases in which the random time instants or their statistics are not known or not reliable. If the sampling irregularity is caused due to the lack of sensor synchronization in the network, several algorithms can ensure a common timescale (Sivrikaya and Yener, 2004), at the expense of additional investments or energy use. Another approach, believed to be largely used in practice, is to disregard the irregularities, assimilating the measurements as soon as possible (Kwok et al., 2004; Huck et al., 2011). In this case, additional noises are tuned in the estimation process, but it might be irrelevant to the overall performance.

Knowing to what extent the estimation accuracy is deteriorated by ignoring the additional uncertainty caused by the sampling irregularity is important to decide whether or not to invest in synchronization. In addition, the investment in more sensors to the network in order to improve accuracy might not pay off, if it increases the occurrence

of irregularities. However there are no detailed studies on the behavior of the degradation in accuracy due to neglecting the irregularity in the sampling process. Therefore, this work assesses the differences in state estimation performance for systems sampled at random time intervals with and without time-stamp for different scenarios. The purpose is to shed some light on the trade-off for investments in sensor networks and synchronization.

1.2 Problem Formulation

Consider the stochastic nonlinear sampled system

$$\dot{x}(t) = f(x(t), u(t), w(t), t), \quad (1.1)$$

$$y(t_k) = g(x(t_k - \delta_k), v(t_k), t_k), \quad (1.2)$$

where $f: \mathbb{R}^n \times \mathbb{R}^p \times \mathbb{R}^q \times \mathbb{R}^+ \rightarrow \mathbb{R}^n$ and $g: \mathbb{R}^n \times \mathbb{R}^r \times \mathbb{R}^+ \rightarrow \mathbb{R}^m$ are, respectively, the process and observation models, assumed to be known. We assume that for all $k \geq 1$, the observations $y(t_k) \in \mathbb{R}^m$ are available. Process and observation noises, $w(t)$ and $v(t_k)$ respectively, are white, Gaussian, zero-mean and mutually independent, with known covariance matrices. The first two moments of the initial random state vector $x(0)$ are also known. Input data $u(t)$ are available at regularly spaced time intervals T , that is $u(iT) \in \mathbb{R}^p, \forall i \geq 1$ are known.

Observations are taken at random time instants t_k and are considered to be sorted ($t_{k+1} > t_k, \forall k \in \mathbb{N}^+$) and defined by the time intervals $h_0 \triangleq t_1, h_k \triangleq t_k - t_{k-1}, \forall k \geq 1$. In this work, we assume that the observation time instants t_k are given by a Poisson random process. In other words, the time intervals h_k are independent and identically distributed (i.i.d.) exponential random variables (RVs) with a known rate parameter λ_h , that is $h_k \sim \mathcal{E}(\lambda_h)$. Since the expected value of an exponential RV is the inverse of its rate parameter, λ_h will sometimes be referred to as expected or average sampling rate of the irregular sampled quantity. An example of time intervals produced by such a random process is illustrated in Figure 1.1. This sampling model characterizes a common application for an event-based sampling scheme or for a networked control system with unsynchronized sensors. (Micheli and Jordan, 2002) consider a set of N identical sensors measuring the state variables of a physical process every L seconds. They

prove that, if the sensors are independent and unsynchronized and N is large enough, then the waiting time between the realization of two consecutive measurements can be approximated by an exponential random variable $\mathcal{E}(\lambda)$, where the parameter is given by $\lambda = N/L$.

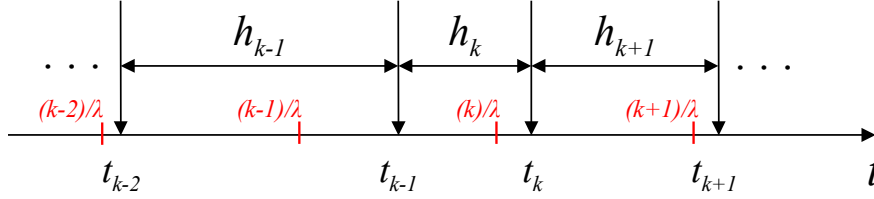


Figure 1.1: Irregular sampling process modeled by a Poisson random process. Regularly spaced time intervals $1/\lambda$ are shown in red. An example of time instants t_k realization is also shown, with the respective random time intervals h_k . The expected value of time interval is given by $E[h_k] = \frac{1}{\lambda}$.

Arrival times to the estimator may be delayed during transmission by a random time amount δ_k , also given by exponential random variables, with parameter λ_{δ_k} , according to Figure 1.2. Out-of-sequence measurements (OOSM) are not considered in this work. We assume that, in case a measurement delay is so big that its packet arrive later than a future measurement, it gets lost in transmission.

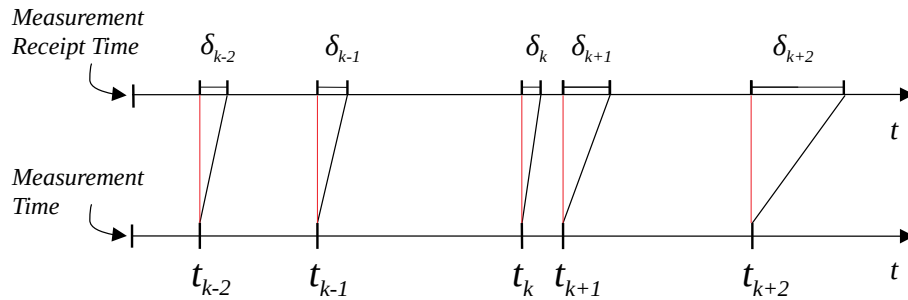


Figure 1.2: Randomly delayed measurements, modeled as exponential random variables. Random measurement times t_k are received by the estimator after a random delay δ_k

When time-stamp information is available, data assimilation can be performed at the correct measurement instants t_k . When they are not, the assimilation moment is

considered to be the random receipt time instant or the next estimation moment, when there are no transmission time delays.

We wish to estimate the state vector $x(t)$ and its covariance recursively, at regularly spaced time intervals T , given their initial values x_0 and P_0 , the process (1.1) and observation (1.2) models, the input or control signals, $u(iT) : iT \leq kT$, and the set of past observations, $y(t_k) : t_k - \delta_k \leq kT$. The knowledge of the time intervals $h_{k-1} : t_k - \delta_k \leq kT$ is also taken into consideration when time-stamp information is available. We assume that the average time interval of observations $1/\lambda_h$ is greater than or equal to T by a factor $\alpha \geq 1$, such that $1/\lambda_h = \alpha T$.

1.3 Objectives

Falta objetivos

1.4 Text Outline

This text is organized in six chapters, including this one. Chapter 1 presents an introduction to the object of study, with an overview of the motivations and historical perspective of the theme, objectives and problem formulation.

Chapter 2 presents a review of the sensor fusion field of science, addressing not only the definitions and taxonomy, but also the advantages of combining information from multiple sources. From the four categorization models of the data fusion problem, the one based on data challenges is further explored. We then introduce and discuss the methods proposed in literature to handle imperfect data.

Chapter 3 discusses the data-related challenges that arise for sampled-data systems, regarding sampling irregularities. Diagrams are built to organize the types, effects and causes of irregularities. We describe the necessary modifications to state estimation observation models, in order to handle such abnormalities in sampling schemes. To perform effective state estimation in the presence of sampling irregularities, methods depend on the knowledge of the exact time measurements were taken. Therefore, we explore time synchronization methods suited for sensor networks.

After the literature review, we focus on the probabilistic sensor fusion approach to sampled-data systems with sampling irregularities. The study of the impact of

neglecting time-stamp information is performed.

Chapter 4 describes the methods used for simulation, considering the adaptations for the scenarios with and without time-stamp. We describe the filtering algorithm and the assumptions used for each scenario. Furthermore, we define the performance metrics used for the results assessment.

In Chapter 5 we present simulated results from two systems: an arbitrary linear system and a unicycle position estimation system. Signal parameters are varied to assess the impact in performance of both considering and not considering time-stamp in estimation algorithms. Performance is evaluated using estimated state errors and estimation consistency.

Finally, we conclude the study in Chapter 6, highlighting the study limitations and suggestions of future work, apart from evaluating if the proposed objectives were achieved.

Sensor Fusion

In this chapter, we review sensor fusion techniques, advantages and terminologies. We start with a brief explanation on the motivations of this field of science, grouping them in two main categories: data authenticity and data availability. We continue with a definition of sensor fusion and an exploration of the available fusion methods classification models. The categorization based on data challenges, that is uncertainty, imperfection, inconsistency and disparateness, is further discussed. We also present data fusion methods that handle imperfect data, which is the most fundamental problem present in information. We end the chapter focusing on probabilistic fusion methods for sampled-data systems.

2.1 Contextualization

The idea that combining information from multiple sensors to improve overall system performance has been in discussion for several decades. In the early days, there were those who argued against the synergism hype that was being spread in military systems, using the multi-sensor concept (Fowler, 1979). In his work, Fowler created what he called his seventh law:

"Be wary of proposals for synergistic systems. Most of the time when you try to make $2 + 2 = 5$, you end up with 3... and sometimes 1.9"

Although he was right to affirm that the added complexity and high costs are not always worth it - especially back then, when devices were more expensive - many posterior studies advocated that the fusion of sensor data will always be better, in the sense that the probability of correctly classifying a target increases. A direct answer to Fowler's work came in the year after (Nahin and Pokoski, 1980), when Nahin and Pokoski used strict concepts and definitions to prove that the addition of sensors improves network performance, but also acknowledged their assumptions of discarding

complexity and costs for the sake of their arguments. This topic continued to draw scientific attention throughout the years, like the work of (Rao, 1998) and (Dasarathy, 2000). Rao focused on fusion methods and its comparison to classifiers' performance. He also established conditions that guaranteed that the fused system will at least perform as good as the best classifier. Dasarathy's work extended that of Rao's, but it was able to describe a certain scenario at which a two-sensor scheme outperforms a three-sensor architecture from a parametric fusion benefits domain perspective. In order to compare performances of fusion levels or algorithms and assess possible benefits of sensor fusion, (Theil et al., 2000) discussed three measures of performance (MOP), one for each sensor management process, which are detection, tracking and classification.

Despite all philosophical discussions, many real applications have been taking advantage of sensor fusion benefits since its advent, like remote sensing (Foster and Hall, 1981), robotics (Richardson and Marsh, 1988) and intelligent systems (Luo and Kay, 1989). Recently, with the modernization and popularization of sensors, its use has grown significantly, with hot topics emerging in the area, such as body sensor networks for health-care applications (Gravina et al., 2017), artificial intelligence (Safari et al., 2014; Jordao et al., 2018) and smart grids (Liu and Wang, 2012; Kordestani and Saif, 2017). Recent reviews of the state of the art (Khaleghi et al., 2013; Jing et al., 2013) provide a very broad understanding of the field and its advances.

We continue this chapter advocating for the benefits of sensor fusion in Section 2.2, describing its motivations and advantages. In Section 2.3, most of the taxonomies used in the area are discussed. We end the chapter with a further discussion on the aspects of data fusion related to imperfect data.

2.2 Motivation and Advantages

Whether or not all sensor fusion approaches outperform the use of less sensors in every aspect for any given condition, the fact is that many fields of science and engineering have been benefiting from choosing the fusion approach.

The reasons why one chooses to fuse information from different sources are various. The works of (Hall and Llinas, 1997; Elmenreich, 2002; Andler and Brohede, 2009; Khaleghi et al., 2013) provide a detailed study on the motivations and advantages of multi-sensor data fusion techniques. A common benefit from the use of multiple

redundant sensors, for instance, is the increase in accuracy. By averaging all the measurements, the expected error decreases by the rate of $(\sqrt{n})^{-1}$, where n is the number of homogeneous sensors, in case of the presence of i.i.d Gaussian noises. In Figure 2.1 different probability density functions (PDFs) with different standard deviations - thus different expected errors - are shown for various quantities of random variables being averaged.

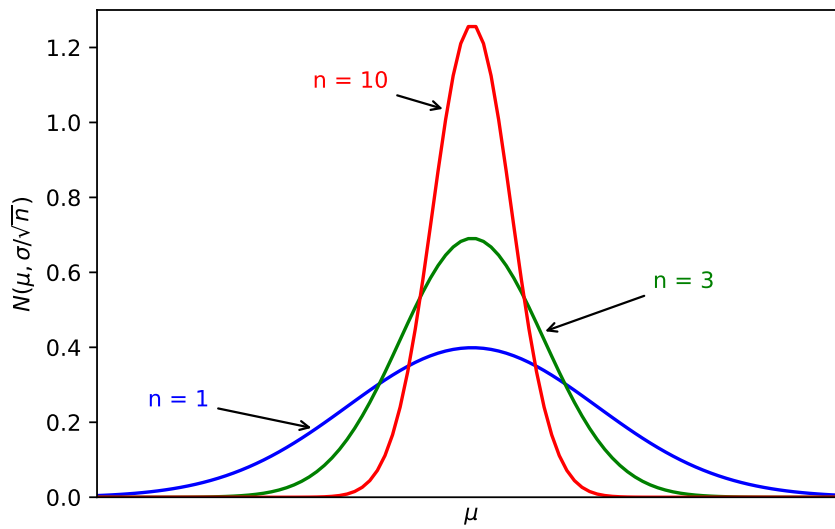


Figure 2.1: Probability distribution functions for different amount of fused measurements, obtained by 1 (blue), 3 (green) and 10 (red) redundant sensors, considering i.i.d additive Gaussian noise. The higher the value of n , the lower is the standard deviation, thus the lower is the expected measurement error.

There are many other reasons to fuse information from multiple sensors. (Elmenreich, 2002) provides an interesting example to illustrate some of them. Imagine a car parking assist system with only one distance sensor mounted at its rear, with limited precision and considerable update time (sampling interval). Now picture how would be the system's performance, considering that the sensor may suffer from: deprivation or occlusion, in the sense that it could be blocked by some physical barrier; coverage, both in spatial and temporal contexts, since it can only sense objects in front of him (spatial) and can only provide information periodically (temporal); precision, with measurement errors being liable to be the cause of unexpected bumps; and uncertainty, when an object, such as a small bicycle, might be missed by the sensor even in the

presence of valid signal. The system would definitely perform at insufficient levels. All these issues could be solved by adding multiple sensors to the architecture.

Based on the studies from Hall, Elmenreich and Andler, we can group most of the advantages in two categories: *authenticity* and *availability* improvements. The first group refers to those benefits that improve the quality of the measurement, whereas the second one encompasses those benefits regarding ranges or data dimensions. The set of multiple sensors can also be of different types (*heterogeneous*), or of the same type (*homogeneous*), with redundant measurements. There may be benefits that are exclusive to the addition of different sensors, others exclusive to the addition of redundant sensors and those that can happen both ways. Figure 2.2 presents a schematic with the different advantages expected in sensor fusion.

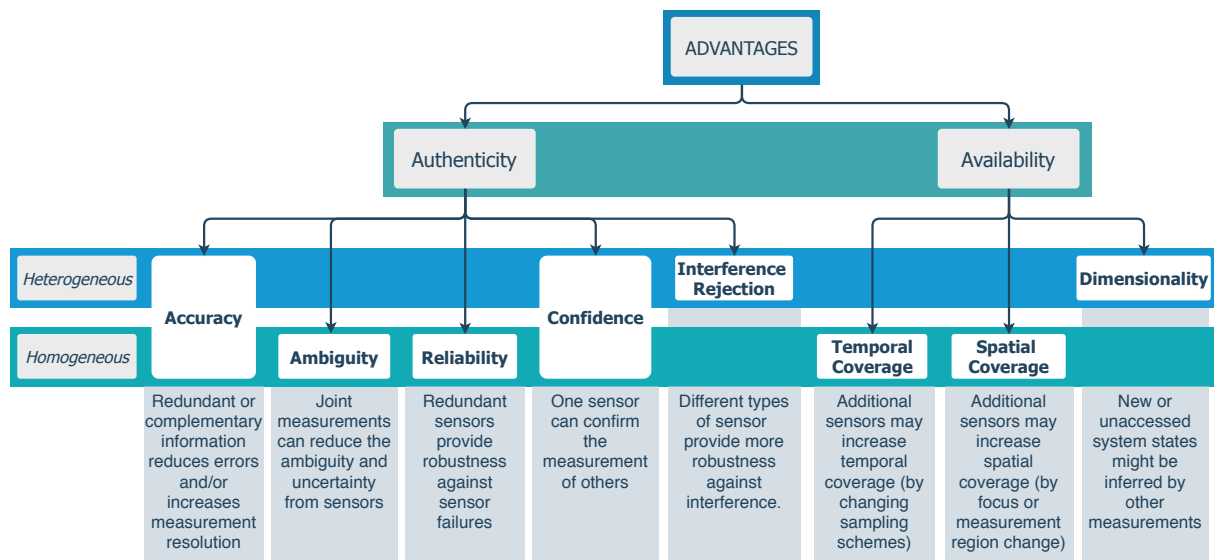


Figure 2.2: Sensor fusion categorization hierarchy based on expected advantages. The white boxes represent the advantages grouped two ways: between authenticity or availability improvements; and between heterogeneous, homogeneous or both sensor architectures

2.3 Taxonomy and Classification

Sensor fusion definitions have evolved throughout the years. The work of (Boström et al., 2007) analyses more than 30 papers on this matter, to propose a more comprehensive and precise definition to the broad area of information, data and sensor fusion, which we reproduce here:

"Information fusion is the study of efficient methods for automatically or semi-automatically transforming information from different sources and different points in time into a representation that provides effective support for human or automated decision making."

Researchers in the field made additional efforts to categorize the fusion techniques, using different approaches. One of the earliest attempts comes from (Durrant-Whyte, 1988), where he considered the dynamic use of information in the fusion processes, creating the so-called dependence model, which grouped sensor fusion in three categories: *competitive*, *complementary* and *cooperative*. Competitive type occurs when multiple sensors measure the same properties, usually referred to as redundant architecture. Complementary fusion describes the scheme of different types of sensors measuring different information about the same global object or feature, enabling a more complete fused information, like multiple cameras covering a large area. And the last category, cooperative fusion, happens when more complex data are combined to provide information that would not be available (or hard to obtain) otherwise. An example would be multiple measurements being processed to create soft sensors. An illustrative schematic is presented in Figure 2.3. An abstraction from the human sensory system to Whyte's model can be done by understanding the way flavors are perceived by our taste and smell sensors, tongue and nose, respectively, in a cooperative fashion, while our both eyes or our both ears perform some sort of complementary fusion.

Another common way to categorize sensor fusion is by the *three-level hierarchy* based on input and output characteristics, which depends on the processing stage at which information is fused. The lower-level is related to *raw-data fusion*, where signals from sensors are combined. The mid-level is usually related to *feature fusion*, where information about characteristics of the object are used in the process. The higher level involves *decision fusion*, that can be understood as a reasoning process, like the methods of evidential belief or fuzzy logic. (Dasarathy, 1997) extended this terminology, proposing five fusion modes, according to Figure 2.4. *Data in - data out fusion* (DAI-DAO), the lowest level fusion, processes raw data and outputs raw data, but with some improvements, such as increased accuracy. *Data in - feature out fusion* (DAI-FEO) extracts features from raw data to describe characteristics of the measured environment. *Feature in - feature out* (FEI-FEO) aims at the refinement of the features entering the process, similarly to what DAI - DAO does to raw data. *Feature in - decision*



Figure 2.3: Classification of data fusion based on sensor interaction. The lower green boxes represent the states or objects being measured. Their properties can be observed directly (straight lines) or indirectly (curved lines) by sensors indicated by the letter S. After fusion, the output information is presented in the red hexagons. Adapted from (Elmenreich, 2002).

out (FEI-DEO) usually performs classification based on a set of features received as inputs. *Decision in - decision out* (DEI-DEO) outputs a better global decision based on local, restricted decisions. Using our human brain data fusion analogy, many examples can be framed into Dasarathy's terminology. The processing of raw signals, such as letters symbols, into features such as words and texts can be interpreted as DAI-FEO fusion. On the other hand, the process of assimilating features of objects from our eyes and ears, and fusing them into a decision about what they are, for instance, can be perceived as an example of FEI-DEO fusion.

The work of (Castanedo, 2013) provides a comprehensive review of these and other classifications of data fusion techniques. His efforts went beyond as he proposed an interesting new approach, based on the type of architecture, summarized in Figure 2.5. In his model, fusion techniques that collect all measurements in a central processor lie on the *centralized* architecture category. Assuming perfect data alignment and association, such scheme should be optimal. However it is keen to many sampling irregularities issues and might provoke network congestion. When a network of nodes is used, each with its own processing capability, the architecture becomes *decentralized*. Such modular



Figure 2.4: Input and output model categorization, representing type of input in green, the method in yellow and the output in red. The fusion levels are shown in the curly brackets.

strategy ensures scalability, since there are no limits to centralized bottlenecks, and survivability to the loss of a particular sensing node. However it can greatly increase communication costs. The third and last configuration is the *distributed* architecture, where each data association is performed by local nodes. The separate outputs are then transmitted to a fusion node, that processes these locally obtained estimates to produce a fused global estimate. This scheme will reduce both the communication costs from decentralized architecture and computational costs from the centralized one, while lacking some of their benefits. A fourth architecture could be defined as *hierarchical*, which combines decentralized and distributed schemes, performing fusion at multiple levels. Getting back to our human sensory capacity, a very complex hierarchical architecture would best describe our brain fusion scheme in Castanedo's classification.



Figure 2.5: Sensor network architectures for data fusion: *centralized*, *decentralized* and *distributed*. Sensors are shown in green circles and the arrows represent the information flow.

A final note on the taxonomy of data fusion methodologies will be given to the work of (Khaleghi et al., 2013), due to its connections to sensor fusion in the presence of irregularities, like the ones that will be discussed in Chapter 3. The idea was to study the methods based on data characteristics that make data fusion a challenging task. The authors referred to these aspects of data as data-related challenges and

categorized the methods by which challenges the methods address. An overview of the challenge hierarchy proposed by the authors is presented in Figure 2.6, with four main categories of how challenging input data can be: *imperfect*, *correlated*, *inconsistent* and *disparate*. The most fundamental problem present in data is imperfection. Indeed, most of the algorithms framed in the other three categories are basically methods that try to neutralize, avoid or minimize their aspects, so that imperfection is the only thing left on data. When correlation is present on data, for instance, the requirements for typical fusion algorithms, such as the Kalman Filter, are broken, so there are methods to eliminate correlation or to minimize its effects, given certain assumptions. In case of data inconsistency, due to outliers, one can act on the sensor outputs directly, to validate information or to detect and remove them automatically. If there are out-of-sequence measurements (OOSM) in data, a type of inconsistency, then the usual frameworks would be: to ignore; to reprocess or use backward/forward prediction; and to augment the state matrices in order to incorporate delayed measurements. Conflicted and disparate data are more specific and are beyond the scope of this study.



Figure 2.6: Categorization based on data challenges hierarchy. For imperfect data, fusion methods and the issues they deal with are also presented.

2.4 Fusion of Imperfect Data

Being the most fundamental and common challenge present on data, imperfection is also the main focus for research in the area. Based on Khaleghi's classification, imperfection on data can be manifested as uncertainty, imprecision and granularity. We can distinguish uncertainty and imprecision with two information examples: *I believe Maria is one point eight meter tall; I am sure that Maria is tall*. In the first sentence, the information is precise, but uncertain. In the second, the information about Maria's height is certain, but imprecise, with some vagueness (fuzziness) attached to it. Usually the amount of precision in data is inversely proportional to the level of certainty. urce of imprecision can also be ambiguity, as in the phrase: *Maria gave birth to her daughter yesterday at 5*. We don't know if it was 5 PM or 5 AM, though the information was certain. The last type of imprecision would be for incomplete data, when we have missing information. The sentence "*Maria's height is above one point five meter*", is incomplete, for example, meaning that only one bound was given. Any height above one hundred and fifty centimeters is possible and any height less than or equal to it is impossible, defining the so-called possibility measures. Finally, granularity is an imprecision related to the internal structure of data, referring to the capacity of distinction among states. Different attributes on the data or a different set of possible states will generate different levels of imprecise information.

Given the amount of potential problems in data and their particularities, it is only natural that no data fusion approach alone could tackle all of them. Researchers have proposed various approaches that focus on one or a few of these issues and (Khaleghi et al., 2013) explore methods for all the challenges in their categorization model. In this study we will limit ourselves to imperfect data, for which, in most cases, the mathematical background of the algorithms relies on the representation of imperfection. These methods are highlighted in Figure 2.6 in different colors and covering one or multiple aspects. In the next subsections we will explore them. Table 2.3 presents a summary of all methods with their main advantages and limitations, adapted from the study of Khaleghi and his coauthors.

2.4.1 Probabilistic

Uncertainty is the most natural source of data imperfection and it is usually modeled by probability density functions (PDFs). Thus, probabilistic fusion methods are the most adequate to handle it. The most classical approach to fuse data based on uncertain measurements is using Bayes' theorem. The idea is to update the probabilities of an hypothesis H given some evidence E by using his famous equation (Stone, 2013)

$$\rho(H|E) = \frac{\rho(E|H)\rho(H)}{\rho(E)}, \quad (2.1)$$

where $\rho(H|E)$ represents a conditional probability, that is the probability of H being true, given E . We can interpret (2.1) as a fusion of *a-priori* belief of an hypothesis ($\rho(H)$) and some current evidence ($\rho(E|H)/\rho(E)$) to come up with a better current estimate of the hypothesis ($\rho(H|E)$).

In addition to Bayes' contribution, Gauss' least squares methods and Fisher's maximum likelihood estimation are the foundations of all probabilistic approaches to data fusion, recursive filtering and state estimation. (Kolmogorov, 1962) in 1941 and (Wiener, 1949) in 1942¹ independently designed a linear minimum mean-square estimation technique, that is considered to be the first probabilistic designed filter, the so called Wiener-Kolmogorov filter. A few years later, perfecting the work of its predecessors, (Kalman, 1960) developed the recursive mean-square filter, a groundbreaking method known as Kalman Filter (KF). Its impact was so big, that only one year after its publication, Kalman's algorithm was used in the Apollo Project (Mohinder and Angus, 2010), to solve its guidance and navigation problem. A review on the evolution of least-squares estimation theory is provided by (Sorenson, 1970).

When it comes to a multi-sensor system, (Willner et al., 1976) introduced three approaches for the discrete Kalman Filter: parallel, sequential and data compression filters. In the parallel filter, all measurements are processed by a KF in parallel, producing a multi-output estimation. For the sequential filter design, multiple KFs are used, where the estimates of a predecessor KF are used as input for the successor KF. Data compression or output fusion filter design compresses similar data using their noise covariance matrix beforehand and the fused output is used as the measurement for a single KF. A fourth method was proposed by (Singer and Kanyuck, 1971), referred to

¹Their discoveries went public a few years later due to secrecy during war times.

as track-to-track fusion (TTF), that employs single-output KFs and fuses their outputs considering the correlation between them.

2.4.2 Evidential Belief

A different framework for managing imperfection is based on Dempster-Shafer evidence theory (DSET) (Shafer, 1976). Shafer argued that his theory, extended from Dempster findings, includes the Bayesian approach as a special case of evidence combination or information fusion. The difference between both relies on the assignment of uncertainty. Whereas Bayesian framework considers one multi-variable PDF to represent each state's uncertainty and the respective covariances, evidential belief theory assigns uncertainties not just to the states, but also to all its possible subsets, using probability mass functions. Imagine the example of Maria giving birth and the information about the time it happened. We can assign uncertainties to the ambiguous possibilities "5 PM" and "5 AM", in order to use the data. If the uncertainty about the information was also an aspect of the data, evidential belief approach could handle it likewise.

Therefore, DSET can be more adequate when fusion takes place at a higher-level estimation, that is the decision-level, referring back to the input and output classification model from Figure 2.4. Situations related to risk assessment configure classical applications (Srivastava, 2011), where we have features or local decisions as inputs, usually with ambiguous and conflicting information and we need to take a global decision out of it.

2.4.3 Fuzzy Logic

Fuzzy logic, first proposed by (Zadeh, 1965) is ideal to handle vagueness in information. Unlike classical crisp definitions, where an element x belongs or not to some definition A , fuzzy sets are characterized by a *membership function* $\mu_A(x)$ which associates a degree of pertinence of x in the interval $[0, 1]$ in A . That is, the closer $\mu_A(x)$ is to the unity, the higher is the grade of membership of x in A . Instead of defining tall people as those with height above certain crisp lower bound, we can define a membership function that assigns continuous degrees of "tallness" to different people. Zadeh also generalized the crisp set notion of operations to the fuzzy set theory: fuzzy complements (NOT), fuzzy intersections (AND) and fuzzy unions (OR).

Vague data can be then fused using fuzzy inference systems (FIS), mapping input variables into an output space using fuzzy logic operators through a set of If-Then fuzzy rules. Two of the most widely used FIS are the Mamdani-type (Mamdani and Assilian, 1975) and Sugeno-type (Sugeno, 1985). The main difference between both is that the outputs of the former rules are also a fuzzy set, while the outputs of the latter rules are polynomials with respect to the input variables. Mamdani and Sugeno-type rules are given, respectively, by

$$R_i^{Mamdani} : \text{If } x_1 \text{ is } A_{i,1} \text{ and } x_2 \text{ is } A_{i,2} \dots \text{ and } x_n \text{ is } A_{i,n}, \text{ Then } y_i \text{ is } C_i, \quad (2.2)$$

$$R_i^{Sugeno} : \text{If } x_1 \text{ is } A_{i,1} \text{ and } x_2 \text{ is } A_{i,2} \dots \text{ and } x_n \text{ is } A_{i,n}, \text{ Then } y_i \text{ is } f_i(X), \quad (2.3)$$

where $x_j \in \mathbb{R}$, $\forall j = 1, \dots, n$ is the j^{th} input variable, $A_{i,j}$ is the j^{th} antecedent fuzzy set for the i^{th} rule, C_i is the consequent fuzzy set for the i^{th} rule, $f_i(X)$ is the output polynomial with respect to the input vector X .

Therefore, we can understand the inference process as a series of steps, according to Figure 2.7. First, we fuzzify the inputs via membership functions. Then we apply the logic operators defined by each rule and find the result implication on the consequent. Finally we aggregate the consequents across all rules and defuzzify its result.

Fuzzy set theory differentiates itself from probabilistic and evidential reasoning theories by modeling the fuzzy membership of a state whose class is ill-defined, whereas the other methods model uncertainties in well-defined state classes.

It is possible to combine fuzzy theory with DSET to handle the imperfections that both approaches can deal with, that is uncertainty, ambiguity and vagueness all together, using the fuzzy evidential belief framework.

2.4.4 Possibilistic

Thirteen years after developing the mathematical background of fuzzy information, Zadeh introduced the concept of possibility theory (Zadeh, 1978), using fuzzy sets as its basis. According to him, fuzzy sets are to possibility theory what measures are to probability.

A membership function $\mu_A(x)$ of a fuzzy set A of a universe of discourse X can be interpreted as the compatibility of x with the concept labeled as A . Letting U be a variable that takes values in X , we can define the *possibility function* π_x of x associated

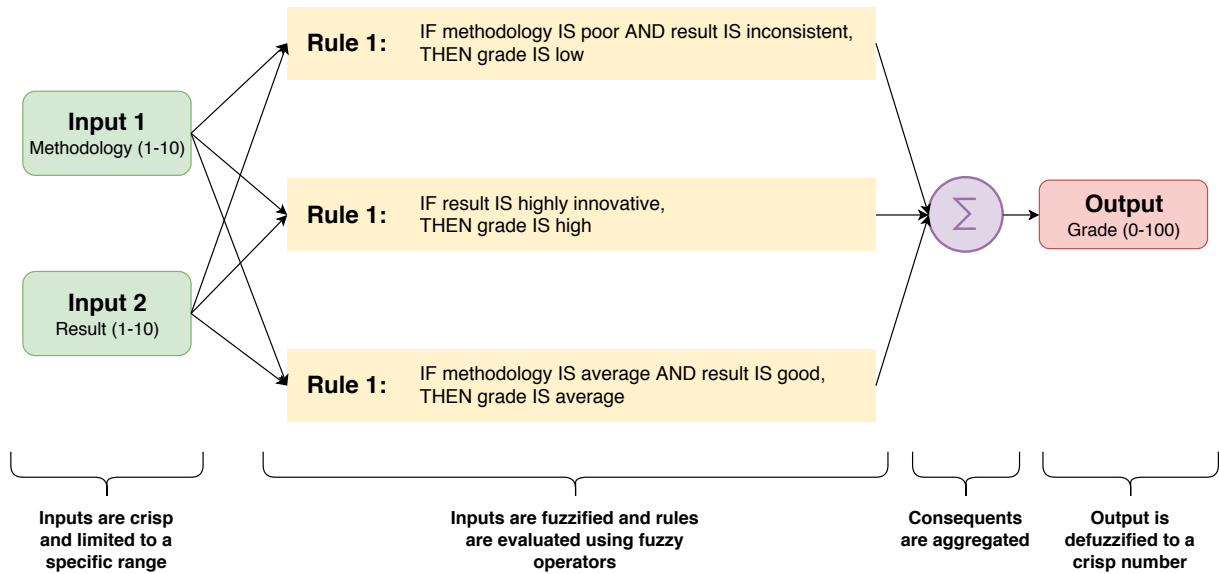


Figure 2.7: Fuzzy inference system example for grading thesis. There are two inputs: methodology and result. They are fuzzified according to the antecedent membership fuzzy sets: poor and average for methodology; and inconsistent, consistent and highly innovative for result. After evaluation of the rules, the implication on the consequents are calculated, producing output fuzzy sets, that are finally aggregated. The final output is then defuzzified to produce a crisp number for the grade, between 0 and 100.

with U to be equal to the membership function of A , that is $\pi_X(u) \triangleq \mu_A(x)$. The interpretation, however, is that the closer $\pi_X(u)$ is to the unity, the more plausible that value is to be true.

Another way to understand possibility functions is in its comparison to density functions in probability. In the information "Maria has failed a few times in the Digital Control course", let us consider X as the number of times in the universe $U = 1, 2, 3, \dots$. The membership function $\mu_A(x)$ can model how close to "a few times" is the fuzzy variable x . From such model, we also define the possibility function $\pi_X(u)$ that can be interpreted as how possible it is that Maria has failed u times in that course. We could also model such lack of information in data by a probability function $\rho_X(u)$, as in how likely it is for Maria to fail u times. Let us consider that an educated set of criteria was employed to define the discrete values of both functions as shown in Table 2.1

Note that according to Table 2.1 it is perfectly possible for Maria to have failed 1, 2, 3 or 4 times. The degree of possibility decreases for higher values and there is an upper bound, from which Maria would have been expelled. On the other hand, based on recent flunk history, the most probable number of times for Maria to have failed

Table 2.1: Possibility and probability functions associated with how many times Maria has failed Digital Control

u	1	2	3	4	5	6	7	8	9
$\pi_X(u)$	1	1	1	1	0.8	0.6	0.4	0.2	0.1
$\rho_X(u)$	0.3	0.4	0.2	0.05	0.03	0.02	0	0	0

is 2, whereas since no student failed more than 6 times, the probability that Maria will fail that many is 0. Thus, possibilistic approach can be more appropriate to cope with incomplete data, with missing information about a lower or an upper bound, for instance, in which case it is clear that some values are impossible instead of unlikely.

The fusion approach to possibilistic data models was extensively studied by (Dubois and Prade, 2000) and it is similar to the rules employed in fuzzy fusion. The design of the rules set is based on how plausible the sources of data are.

2.4.5 Random Set

So far, the presented methods are able to cover all aspects of uncertainty and imprecision. Although some of them can tackle multiple aspects, like DSET and Fuzzy DSET, none of them can handle all the sources of imprecision and uncertainty altogether. The random set approach to data fusion, proposed by (Goodman et al., 1997), offers such potential to integrate all these aspects in one unifying structure. The idea was to generalize the single-sensor, single-target statistics (random variables) to a broader multi-sensor, multi-target statistics (random sets), also known as finite-set statistics (FISST). The direct mathematical parallels between them are presented in Table 2.2.

By modeling the system states and measurements as random sets of finite size instead of vectors of random variables, a variety of different phenomena can be described, such as target disappearance or appearance, extended or unresolved targets, missing measurements and false alarms (Khaleghi et al., 2013). As described by (Goodman et al., 1997), the random set approach can model systems that are comprised of randomly varying numbers of randomly varying objects of various kinds.

Mathematically speaking, random sets are random elements whose values are sets. A random set U is a finite set, whose power set $\mathcal{P}(U)$ is composed of elements described by some specific probability law. In other words, it is defined by

Table 2.2: Direct mathematical parallels between single-sensor, single-target and multi-sensor, multi-target. Adapted from (Goodman et al., 1997; Mahler, 2004)

Single-sensor / target	Multi-sensor / target
random vector, Z	finite random set, Σ
sensor	global sensor
target	global target
observation, z	global observation-set, Z
parameter, θ	global parameter-set, Θ
derivative	set derivative,
integral	set integral,
probability measure	belief measure,
prior PDF	global PDF,
likelihood	global likelihood,
information theory	multi-target information theory
filtering theory	multi-target filtering theory

$$f : \mathcal{P}(U) \rightarrow [0,1] \text{ with } \sum_{A \in \mathcal{P}(U)} f(A) = 1 \quad (2.4)$$

where f can be interpreted as a PDF defined on sets rather than on points of U . That is, the probability that the subset A of U is selected is $f(A)$.

Efficient applications of random set theory have been studied in tasks such as system identification and time-series forecasting (Nuñez-Garcia and Wolkenhauer, 2002), target tracking (Maehlich et al., 2006) and econometrics (Molchanov and Molinari, 2014).

2.4.6 Rough Set

Granularity is the only type of imperfection left from the categorization presented in Figure 2.6. It refers to the extent to which objects can be distinguished by data, considering the features or attributes that define them. Additionally, the way a set of features is designed will depend on a given knowledge base. Some objects might be discernible considering one set, but indiscernible in another set. If we choose to characterize a group of people by their age and height, a woman and a man might be

indiscernible. If we add sex to the set of features, they become discernible. For the sensor fusion field, we can think of data being collected in a very refined universe of discourse, while the universe of concepts in which we transform data into knowledge is coarser, and thus some objects in the data might be indiscernible. These indiscernible objects in rough set theory are referred to as *elementary sets* or *elementary granules* for a specific set of features. The union of these *elementary sets* form what is called *definable sets*.

Based on these concepts, (Pawlak, 1991) developed the rough set theory, which enables dealing with different data granularities by means of *approximation spaces*. The idea is to provide crisp lower and upper bounds to undefined sets of objects in a given knowledge base. Let B be a subset of features chosen to describe objects in the universe of A , that is $B \subseteq A$. If there is a target set X that is undefined in B , that is there are objects x in X that are indiscernible by A , its definition can be approximated by two sets (Pawlak and Skowron, 2007)

$$\begin{aligned} B_*(X) &= \{x \in A : B(x) \subseteq X\}, \\ B^*(X) &= \{x \in A : B(x) \cap X \neq \emptyset\}, \end{aligned} \tag{2.5}$$

and

$$BN_B(X) = B^*(X) - B_*(X), \tag{2.6}$$

where x represents elements or objects in the universe of A , $B_*(X)$ and $B^*(X)$ are the *B-lower* and *B-upper* approximation of X , respectively and $BN_B(X)$ is the approximated X , also called as *B-boundary* region. If the boundary region is empty, then the set X is crisp or exact with respect to B , whereas if it is not empty, then the set X is rough with respect to B . Figure 2.8 illustrates an approximate space in which the universe is partitioned into elementary squares for which subset X is undefined, but can be approximated is by upper and lower bounds.

In (Pawlak, 1991) and in the references therein, many real life applications of rough set theory are explored, such as civil engineering, medical data analysis, aircraft pilot performance evaluation, vibration analysis and image processing.

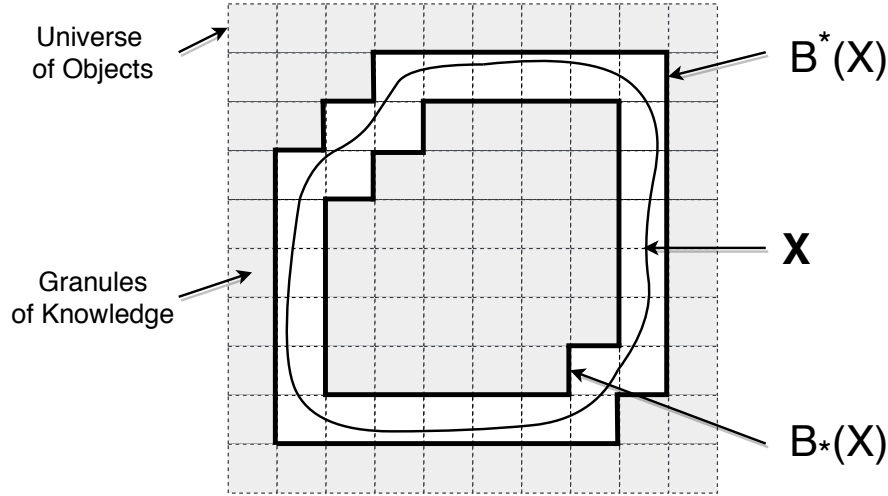


Figure 2.8: Best approximation of the rough set X by lower $B_*(X)$ and upper $B^*(X)$ crisp sets. The elementary granules are squares and the union of these granules form the universe of objects.

2.5 Chapter Summary and Final Remarks

In this chapter, sensor fusion literature is reviewed. We explore the discussion about performance improvement from the combination of information from multiple sources, that has been drawing attention for many decades. The main reasons for the evolution of sensor fusion as a field of science are presented in a comprehensive way, divided by the expected advantages in data authenticity and data availability. We continue with the definition and classification of sensor fusion approaches. Four main taxonomies are reviewed: classification based on sensor interaction; the input/output model based on the three fusion levels approach; sensor network architecture designs; and the categorization based on data challenge hierarchy. The last approach is especially interesting, since it relates to the core of this study: sensor fusion in the presence of irregularities in data. Algorithms that deal with the many aspects of data imperfection are summarized in Table 2.3, such as: probabilistic; evidential belief; fuzzy logic; possibilistic; random set; and rough set theory. Hybrid methods have also been studied in the field, with interesting results.

Being the most popular method in the fusion community, the remaining of our study will focus on probabilistic methods for data fusion and its application on state estimation for sampled-data systems. A new data challenge is often present when complex sensor architectures are used to observe system states: sampling irregularity.

Table 2.3: Data fusion methods for imperfect data, adapted from (Khaleghi et al., 2013, page 35, Table 1)

Algorithm	Approach	Advantages	Limitations
Probabilistic	Bayesian framework to fuse uncertain data represented by probability density functions	Well-established and optimal for certain conditions	Might be unsuited for other data imperfections
Evidential Belief	Data fusion based on probability mass function, using Dempster-Shafer theory and combination rules	Enables fusion of both uncertain and ambiguous information	Incapable of dealing with other aspects of imperfection
Fuzzy Reasoning	Vague data represented by fuzzy set theory and fusion based on fuzzy rules	Intuitive and interpretable approach for vague data, such as human generated	Only applicable to vague data
Possibilistic	Data fusion based on fuzzy theory, with data representation similar to probabilistic and evidential belief	Indicated for poorly informed environment with incomplete data	Not very common and well-established
Rough Set	Imprecise data is approximated based on granularity and manipulated via classical set theory	Dispenses preliminary or additional information	Data granularity must be adequate
Random Set	Extension of Bayesian filter, representing the state space as a random set to capture many aspects of imperfection	Can potentially provide a unified framework for fusion of imperfect data	Not very appreciated by the fusion community
Hybridization	Combination of different fusion methods and data representation	More comprehensive treatment of data imperfection and benefits from complementary fusion	Computational expensive and very problem specific

Irregular Sampling

In the last chapter, we reviewed the main motivations and advantages behind the sensor fusion field of science, as well as its techniques. Despite all the growth and benefits from fusing data from multiple sensors, some challenges naturally appear. For the state estimation problem for sampled-data systems, a common challenge is related to sampling irregularities introduced in the network.

In this chapter, we review the irregular sampling problem. First, the concept of irregular sampling adopted in this study is discussed. In Section 3.2 we categorize the different types of irregularities that may occur in sampling and discuss their main causes and characteristics. Then, in Section 3.3, each irregularity is further discussed, with examples, mathematical models and their subdivisions, where applicable. We end this chapter with a discussion of time synchronization in Section 3.4, which is needed to guarantee a common time scale for all nodes in network, enabling the irregularities to be dealt with appropriately.

3.1 Definition of Irregular Sampling

Most of the systems studied in estimation and control theories take place in an analog environment with dynamics evolving according to continuous-time differential equations. However, due to the many benefits of digital technology implementations, their signal must be sampled in order to be processed, giving rise to the so-called *sampled-data systems*.

In practice, the sampling process is modeled by a sampler and a data hold device, that enables signal reconstruction. The most common data hold configuration is the zero-order holder (ZOH), that locks the signal value at the sampling instant until the next sample is available. Therefore, the output of a sampler that transmits data every T seconds and a ZOH is given by (Phillips and Nagle, 1995)

$$\bar{f}(t) = f(0)[u(t) - u(t - T)] + f(T)[u(t) - u(t - 2T)] + f(2T)[u(t - 2T) - u(t - 3T)] + \dots, \quad (3.1)$$

where $\bar{f}(t)$ represents the reconstructed sampled signal, $f(t)$ is the original continuous-time signal and $u(t)$ is the unit-step function. Taking the Laplace transform of (3.1) we have

$$\begin{aligned} \bar{F}(s) = \mathcal{L}[f(t)] &= f(0) \left[\frac{1}{s} - \frac{e^{-Ts}}{s} \right] + f(T) \left[\frac{e^{-Ts}}{s} - \frac{e^{-2Ts}}{s} \right] + f(2T) \left[\frac{e^{-2Ts}}{s} - \frac{e^{-3Ts}}{s} \right] + \dots \\ &= \left[\sum_{n=0}^{\infty} f(nT) e^{-nTs} \right] \left[\frac{1 - e^{-Ts}}{s} \right]. \end{aligned} \quad (3.2)$$

Only the first term of (3.2) is dependent on $f(t)$ and thus can be interpreted as the sampler, whereas the second term represents the ZOH. Note that neither exists alone, since the real physical signal is composed by both terms. Taking the inverse Laplace transform of the sampler term yields

$$\mathcal{L}^{-1} \left[\sum_{n=0}^{\infty} f(nT) e^{-nTs} \right] = f(0)\delta(t) + f(T)\delta(t - T) + f(2T)\delta(t - 2T) + \dots, \quad (3.3)$$

where $\delta(t)$ is the unit impulse function, also known as Dirac delta function. Although it does not represent a real signal, (3.3) is referred to as the *ideal sampler* (Phillips and Nagle, 1995).

Thus if the state observations of a sampled-data system are transmitted through an ideal sampler, it can be modeled as

$$y(t) = g(x(kT), v(kT), kT), \quad \text{for } kT \leq t < (k + 1)T, \quad (3.4)$$

where $g: \mathbb{R}^n \times \mathbb{R}^r \times \mathbb{R}^+ \rightarrow \mathbb{R}^m$ represents the observation model, $x(kT) \in \mathbb{R}^n$ is the state vector, $v(kT) \in \mathbb{R}^m$ is the measurement error, $k \in \mathbb{N}$ is the discrete-time index and $T \in \mathbb{N}^+$ is the sampling interval.

Therefore, a sampled-data system is regularly sampled if its observation model can be modeled by (3.4), as a consequence of an *ideal sampler*. In other words, in this study we refer to *regular sampling* as measurements being taken periodically, with single-rate and transmitted without time-delay and any loss of information. Anything else will be

framed as *irregular sampling*.

3.2 Contextualization

Sampling irregularities may occur due to a variety of issues. Sometimes they occur as undesired side effects of using large sensor networks architectures and others due to deliberate non-uniform sampling schemes. In this section we try to categorize and review the main irregularities observed in practice. The diagram in Figure 3.1 provides a simplified overview of them, separated by their sources.

Networked system monitoring and control appears to be the main cause of irregular sampling. Unreliable communication channels may lead to random time delays and loss of information, specially if data are transmitted using a common media (Saheb-sara et al., 2007; Moayedi et al., 2011). In case they get randomly interrupted during transmission or if a sensor fails at some point, the signal received may predominantly contain noise, causing uncertain observation or packet dropouts (Hadidi and Schwartz, 1979; Wang et al., 2009). Systems that are observed by a large number of desynchronized sensors will provide observations at random time intervals (Micheli and Jordan, 2002). If they are synchronized but designed to operate in a centralized fashion, there is a chance that different time delays are produced due to distinct transmission routes for each sensor (Bar-Shalom, 2000; Challa et al., 2003; Anxi et al., 2005).

However, the communication networks shall not always be held responsible. Some applications are designed to be measured in an irregular way. In event-based schemes, for example, the measurements are transmitted only when certain conditions are met (Liu et al., 2014; Zou et al., 2017). Such approach can reduce communication resource consumption substantially (Hu et al., 2017), but it will cause aperiodic sampling. Non-Uniform Sampling (NUS) is also intentionally used as an alias detection method (Kunoh, 2015) or to enhance the spectral resolution of signals, largely used in Nuclear Magnetic Resonance (NMR) spectroscopy analysis (Hyberts et al., 2013), for instance. In other situations, due to the nature of the process being observed, the measurement strategy relies on different procedures. For a lot of chemical processes, for instance, the variables can be measured in an online, fast rate and delay free fashion, but providing inaccurate data. Therefore, lab analyses are used to improve estimation quality, but usually at slower rates, sometimes irregularly and with possible time delays (Fatehi



Figure 3.1: Irregular sampling diagram, showing the main causes (in orange) and effects (in blue)

and Huang, 2017). Other industrial applications suffer from the same dilemma, and the sampling scheme ends up with a multi-rate data transmission, with random time delays and possibly measurement scarcity (Peñarrocha et al., 2012).

Finally, sampling irregularities might also appear due to a specific nature of a system. In some high maneuverable target-tracking applications, for example, there is a chance that the sensor misses the target, transmitting only noise, leading to the so called uncertain observation issue (Wang et al., 2009; Chen et al., 2013).

Whatever the reason for the irregularities, data need to be associated in order to

be fused into knowledge. A crucial part of association is temporal synchronization of observations, so that the exact time at which measurements are taken are available (Ping, 2003). Most sensor fusion methods for irregularly sampled systems rely on the correct time-stamps to develop modifications in classical algorithms. If observations are imprecisely time stamped, some alternatives have been proposed (Julier and Uhlmann, 2005; Huck et al., 2011) that incorporate some aspects of that imprecision in the estimation method. Still, some knowledge about the irregularity is assumed to be known. Alternatively, many techniques for time synchronization can be performed, to ensure a common timescale for all the sensors.

On the next sections, we review the main irregular sampling types and the main approaches to deal with time synchronization in sensor networks.

3.3 Types of Sampling Irregularity

3.3.1 Time Delay

Time-delay systems (TDS) are probably the most common mathematical representation to time delays in practice. The works of (Richard, 2003; Fridman, 2014) and the references therein provide a good coverage of the subject. In TDSs, there might be delays in the input or in the output signals, introduced by communication networks, or even in the states themselves. The latter phenomenon is called system with aftereffect or dead-time. Since we are studying the irregular sampling issue, only signal delays are relevant to us. A summary of causes and effects that time delay causes in an estimator are illustrated in Figure 3.2.

Considering delays in the measurement model only, (Lu et al., 2005) studied the estimation problem when they are constant and known. They describe a discrete linear measurement model observed by l different systems with delays as

$$y_i(kT) = H_i(kT)x(t_i) + v_i(kT) \quad (3.5)$$

where k is the discrete-time index of measurements, T is the sampling interval, $i = 0, 1, \dots, l$ and l is the number of different known delays for each observation system. $y_i(kT) \in \mathbb{R}^{p_i}$ are delayed measurements and $v_i(kT) \in \mathbb{R}^{p_i}$, the measurement noise. The known delayed time instants are given by $t_i = t_{i-1} - d_i$, with $d_0 = 0$, $d_i > 0$ for $i > 0$ and



Figure 3.2: Time delay diagram, showing the main causes (in orange) and effects (in dark blue) of time delay irregularity. The light blue boxes indicate different types that lead to different effects.

$t_0 = kT$. For a given time instant kT , $y_i(kT)$ represents the observation of state $x(t_i)$ at time kT , with total delay $\sum_{k=1}^i d_k$. Thus, if $T \geq d_1 + \dots + d_l$, the complete observation vector of state $x(t_i)$ at time kT , becomes $[y_0^T(kT) \dots y_l^T(kT)]^T$. On the other hand, if the sampling interval is smaller than the delay of one or more observation system, that is $d_1 + \dots + d_{i-1} \leq T < d_1 + \dots + d_l$, then observation of the system is given by $[y_0^T(kT) \dots y_{i-1}^T(kT) 0 \dots 0]^T$.

For some systems, delays might not be known and constant, but still multiple of a fixed value. In such cases, observations might be received in a burst, when more than one packet arrive between two consecutive sampling instants. When that happens, the estimator might use only the latest measurement and discard all others, or implement a buffer to iterate over all received packets (Moayedi et al., 2011).

However, in many applications the measurements are received by the estimator with irregular and unknown delays, although taken at regular time intervals. In such cases, time delays can be interpreted as a stochastic process $d(k)$, varying randomly throughout time. (Han and Zhang, 2009) describes a discrete-time measurement model for random delayed observations as

$$y(k) = H(k)x(k - d(k)) + L(k)v(k) \quad (3.6)$$

where $d(k) \in \mathbb{N}$ is a random but bounded time delay, assumed to be a discrete-time Markov Chain with finite space $\{0, d\}$, observable at each sampling time k .

Multiple of a known lag or not, delayed measurements from a multisensor system are subject to arrive disorderly, which leads to the sampling irregularity commonly known as out-of-sequence-measurements (OOSM). It can be classified in three ways, depending on the number of lags, according to Figure 3.3.

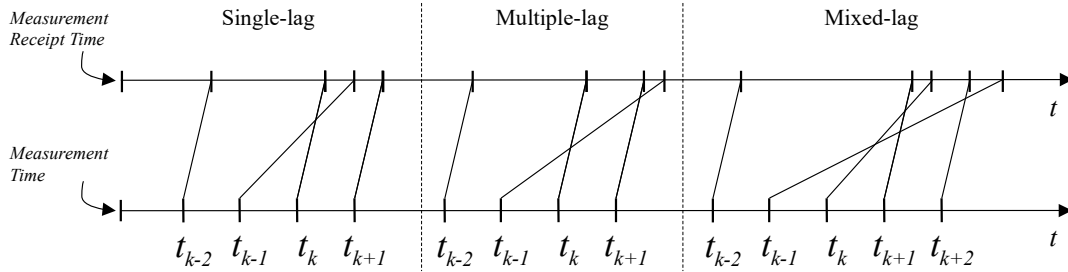


Figure 3.3: Different classes of out-of-sequence measurements irregularities

(Anxi et al., 2005) describes four different filtering approaches to deal with OOSM: reprocessing, that stores filter results to rollback with the time-delayed measurement; data buffering, that holds a set of measurements, greater than the maximum expected lag, to be sorted before filtering; discarding data, that neglects time-delayed measurements; and directly updating, that uses the delayed information to update current state estimate. (Bar-Shalom, 2000) used the last approach to describe an optimal filter for the single-lag case.

3.3.2 Packet Loss

When data are being transmitted by a large network of sensors, there is a probability that they get lost in the way or they might arrive after a significant delay, which is equivalent to a loss for practical applications (Sinopoli et al., 2004). Usually referred to as packet dropout or loss, missing or intermittent observations or scarce measurements (Albertos et al., 2004) they may happen due to node failures, network congestion,

limited bandwidth or temporal failure. A summary of causes and effects that time delay causes in an estimator are illustrated in Figure 3.4.

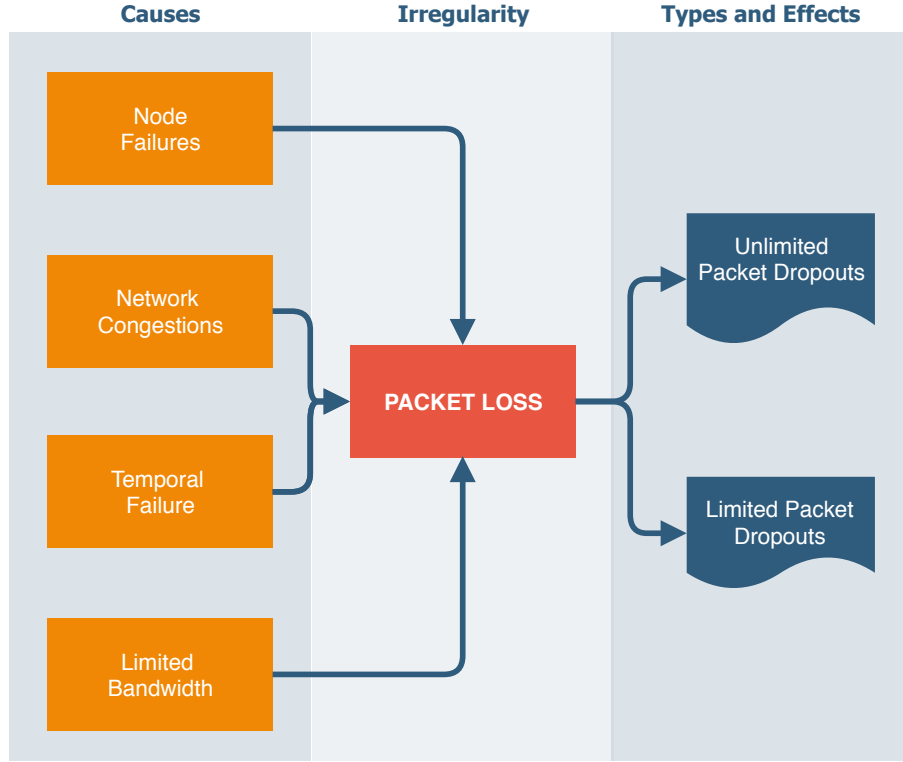


Figure 3.4: Packet loss diagram, showing the main causes (in orange) and effects (in dark blue) of time delay irregularity.

Mathematical description of packet dropouts can be carried out recursively, as described in (Ma and Sun, 2011), by

$$\begin{aligned} z(k) &= H(k)x(k) + v(k), \\ y(k) &= \xi(k)z(k) + (1 - \xi(k))y(k-1), \end{aligned} \tag{3.7}$$

where $z(k) \in \mathbb{R}^m$ is the measured output transmitted to the estimator, $v(k) \in (R)^m$ is white noise, $y(k) \in \mathbb{R}^m$ is the measurement received by the estimator and $\xi(k) \sim \text{Ber}(p)$ is a Bernoulli random variable that takes the value 1 with probability p and 0 with probability $1 - p$. That is, when $\xi(k)$ is 1, there is no packet dropout. If $\xi(k)$ is 0, however, the latest output is used at current time, in a recursive fashion.

Another way of describing multiple packet dropouts is by limiting the amount of consecutive dropouts (Shuli Sun et al., 2008), where the received measurements are

defined by

$$y(k) = \xi(k)z(k) + (1 - \xi(k))\xi(k-1)z(k-1) + \dots \\ + (1 - \xi(k))(1 - \xi(k-1))\dots(1 - \xi(k-N+1))z(k-N), \quad N \geq 1. \quad (3.8)$$

Such a model dictates that the measurement used by the estimator will be only the most recent available, and the amount of missing observations is limited to N . This conclusion can be drawn by the fact that

$$\xi(k) + (1 - \xi(k))\xi(k-1) + \dots + (1 - \xi(k))(1 - \xi(k-1))\dots(1 - \xi(k-N+1)) = 1, \quad (3.9)$$

which means that if the Bernoulli RV realization for the most recent measurement available is 1, all past measurement terms will be multiplied by 0.

3.3.3 Uncertain Observation

For some applications, there is a chance that the observation signal sent to the estimator contains only noise. According to (Jaffer and Gupta, 1971), it happens as a consequence of two situations: the observation was taken, but it was lost during transmission, due to communication failures; or it was not transmitted at all, as it may happen for target tracking systems, for example, when the object being observed is not tracked at a sample time. A summary of causes and effects that time delay causes in an estimator are illustrated in Figure 3.5.

An observation model for a sampled-data system with uncertain observations can be described as

$$y(k) = \xi(k)C(k)x(k) + D(k)v(k) \quad (3.10)$$

where $\xi(k) \sim \text{Ber}(p(k))$ is a Bernoulli random variables, taking values of 0 or 1, with probabilities $p(k)$ and $1 - p(k)$, respectively.

Unlike the packet dropout problem, when the missing data are associated with the total absence of signal, the issue of uncertain observation has to be dealt with differently. A common approach is to detect the existence of signal prior to the assimilation, using a likelihood ratio test. (Middleton and Esposito, 1968) proposes a joint approach to systematically detect and extract information from observation signals. If the estimator and detector are developed separately, the probability of false alarms is not used in



Figure 3.5: Uncertain observations diagram, showing the main causes (in orange) and effects (in dark blue) of time delay irregularity.

the estimator, making it sub-optimal. (Nahi, 1969) developed an optimal recursive estimator, that uses the information of the random variable γ in the algorithm, assuming its sequence is independent and identically distributed. (Hadidi and Schwartz, 1979) generalized the work of Nahi, for the case when the uncertainty of the signals presence is described by a Markovian sequence of binary random variables.

3.3.4 Aperiodic Sampling

All irregularities discussed so far may be present even in a periodic sampling scheme. However, for some applications, the sampling intervals are time-varying due to a variety of phenomena, causing the so-called aperiodic or asynchronous sampling. A summary of causes and types of aperiodic sampling is presented Figure 3.6.

Usually such irregularity happens in networked and embedded control systems, with unpredictable networked-induced issues, such as irregular faults on samplers, oscillated loads, intermittent saturation or even variations in system components or parameters (Shen et al., 2016). Some imperfections may cause what is known as sampling jitter noise, which leads to time intervals being almost uniform. Automotive applications, radar imaging or event controlled systems are a few examples. In such cases, jitter noise happens due to a sampling frequency similar to the clock frequency; to sampling requests delayed by the network; or to imperfect synchronization (Eng and Gustafsson, 2005). For networks with a large amount of unsynchronized sensors,

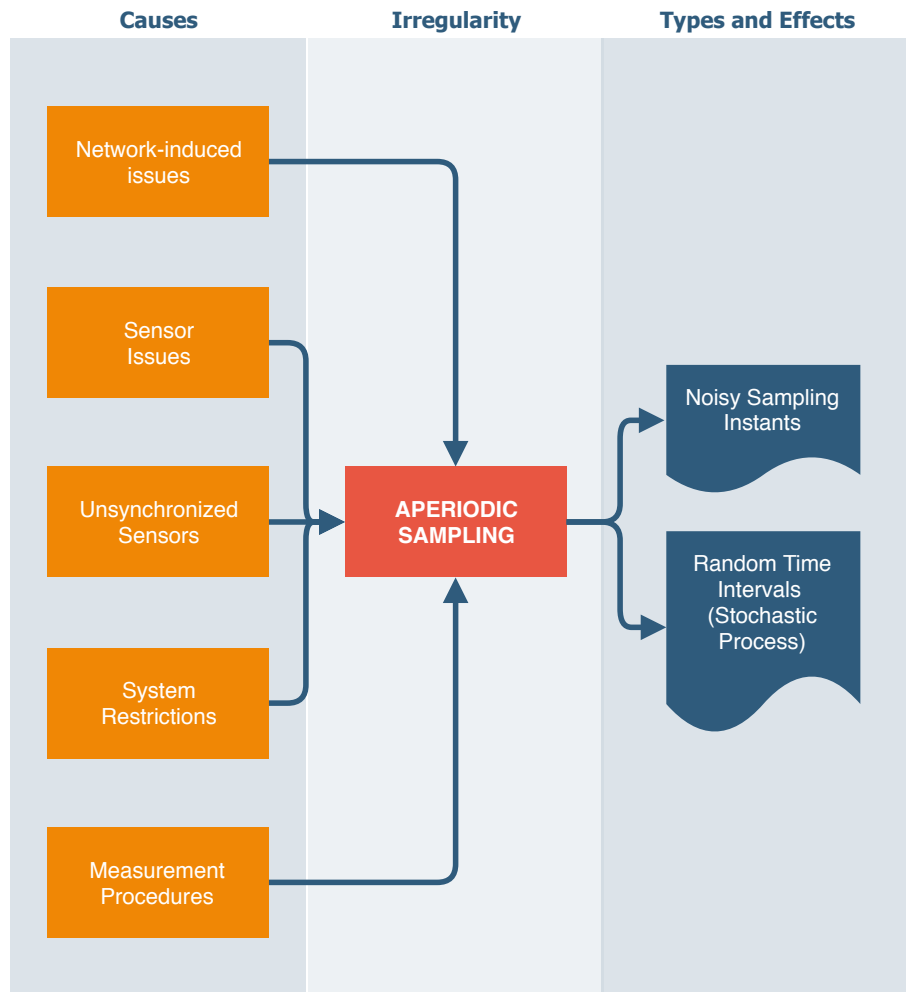


Figure 3.6: Aperiodic sampling diagram, showing the main causes (in orange) and types (in dark blue) of irregularity.

measurement arrival time instants are randomly spaced and can be modeled as stochastic processes ([Micheli and Jordan, 2002](#)). Sometimes, the system being observed has particularities that causes the aperiodic sampling. One example is seismology, where the spatial coordinates are irregularly sampled, because of natural obstacles ([Marvasti, 2001](#)). Other large scale systems, such as power grids, have sensors with huge geographical separations and different communication links to the estimation hub, causing multiple and random inter-observation intervals ([Yan et al., 2017](#)).

Whereas for most cases the deformities in sampling time intervals appear as unwanted effects, there are cases when the sampling rule is designed to work aperiodically. If there are limitations of communication resources (limited bandwidth or computation capacity, for instance) or a need for reduced energy consumption, time-driven

sampling might be neglected in favor of an event-based scheme. In such strategy, an event-triggering mechanism is responsible for determining the sampling instants, according to Figure 3.7. For time-driven schemes, a clock triggers the transmission instants, while event-driven sampling instants depends on the sensor output itself with an optional feedback loop from the estimator, to assess estimation performance. Therefore, the trigger mechanism design provides a trade-off between performance and resource consumption efficiency, attracting a lot of research interest (Liu et al., 2014). The most common strategy for event-driven state estimation is the send-on-delta (SOD) (Miskowicz, 2006), which triggers the transmission when the value of the measured state deviates from the previous assimilated observation by an interval $\pm\Delta$, with $\Delta > 0$. Other strategies were studied in (Zou et al., 2017). To avoid the risk of unexpected high amount of triggered measurements in a short period of time, which can lead to the dreaded Zeno behavior (Tabuada, 2007), lower-bounds can be defined both for the Δ -value or for some explicit minimum inter-event time.

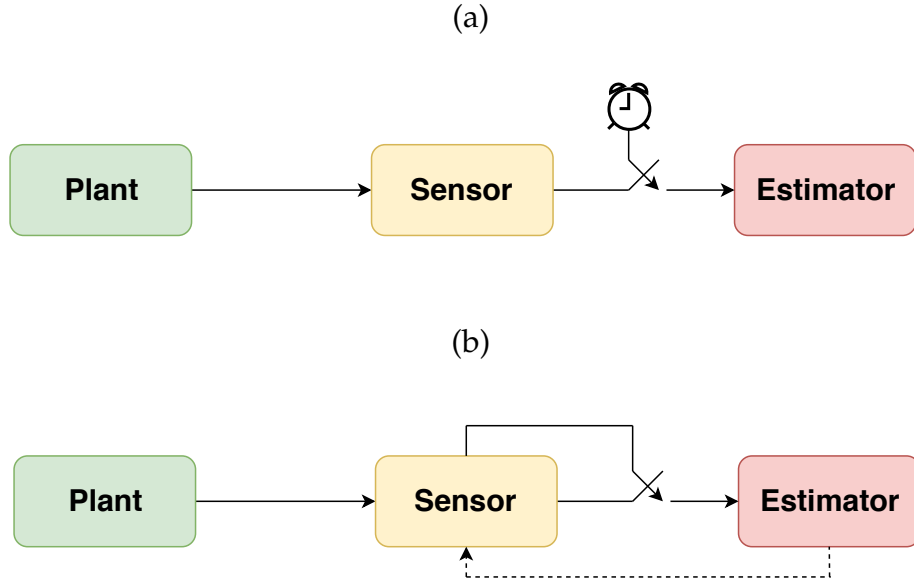


Figure 3.7: (a) Time-driven and (b) event-driven sampling schemes. The connection between sensor and estimator is triggered by different mechanisms.

The measurement model of a linear system with aperiodic sampling can be defined as

$$y(t_k) = H(t_k)x(t_k) + v(t_k) \quad (3.11)$$

where t_k is the random sampling time instant and the observation model matrix $H(t_k)$ is time-varying.

Generalizations of aperiodic sampling can be divided in two categories, based on how the estimator perceives the irregularity: as time noise added to a periodic pattern; or as a stochastic process, according to Figure 3.8.

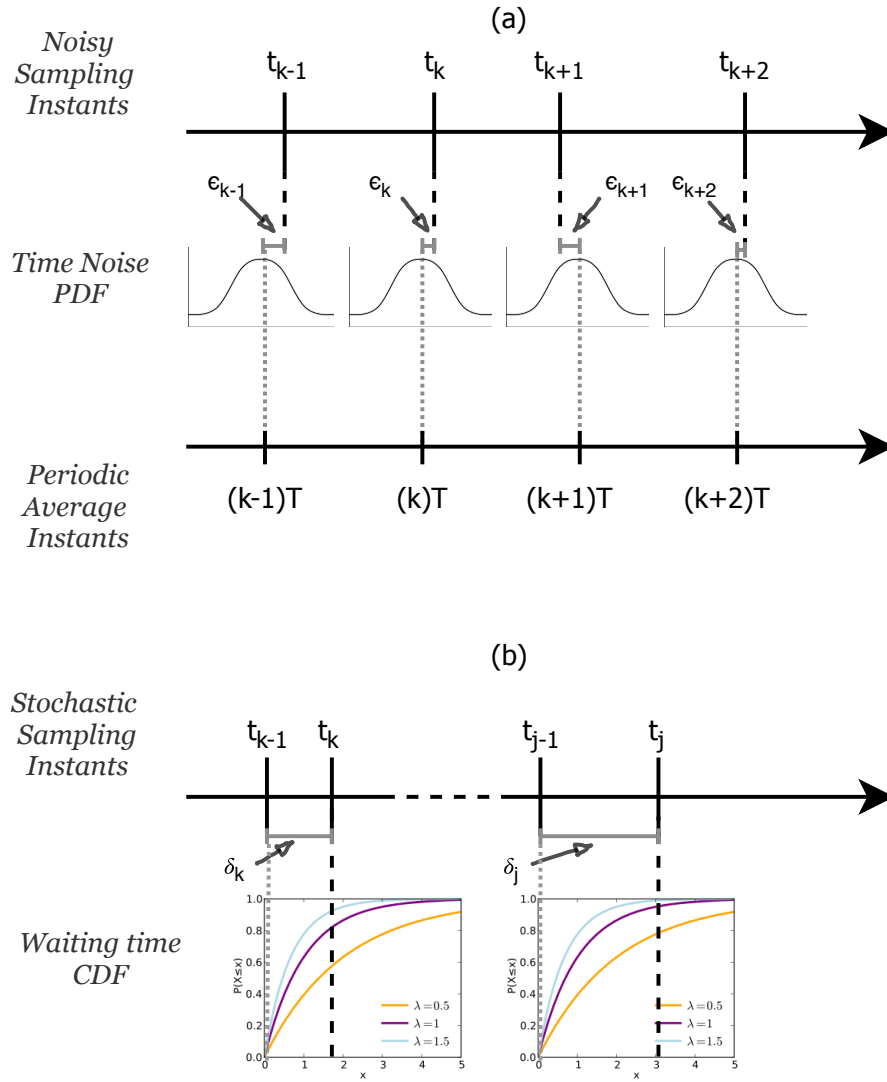


Figure 3.8: Two models of aperiodic sampling: (a) noisy sampling over periodic intervals, with a Gaussian random variable added to expected time instants kT ; and (b) sampling instants modeled as a stochastic process, with time intervals characterized by an exponential random variable. For (b), the cumulative distribution functions are shown, for different λ parameter values.

For the first case, random time instants t_k and the random time intervals δ_k can be

defined as:

$$\begin{aligned} t_k &\triangleq kT + \epsilon_k, \\ \delta_k &\triangleq t_k - t_{k-1} \end{aligned} \quad (3.12)$$

where t_k is the k^{th} sampling instant, T is the periodic time interval and ϵ_k is the deviation from the expected value kT . Note that, if the sampling time instants are a sequence of i.i.d Gaussian random variables, with variance σ^2 , that is $t_k \sim \mathcal{N}(kT, \sigma^2)$, $\forall k \sim \mathbb{N}$, then the time interval random variable is Gaussian, with expected value T and variance $2\sigma^2$, that is $\delta_k \sim \mathcal{N}(T, 2\sigma^2)$.

For the stochastic process generalization, sampling time instants t_k can be defined by the random time intervals δ_k , such as:

$$\begin{aligned} \delta_k &\triangleq t_k - t_{k-1}, \\ \delta_0 &\triangleq t_1 \end{aligned} \quad (3.13)$$

where random time intervals δ_k can be modeled, in the most flexible way, as a gamma probability density function, that is $\delta_k \sim \Gamma(\kappa, \theta)$. If the shape parameter κ is a positive integer, then it becomes an Erlang distribution, as set in (Kanchanaharuthai and Wongsaisuwan, 2002). For the most common case, where κ is held constant, the random time interval δ_k follows an exponential PDF and the time sequence t_k is represented by a Poisson stochastic process (Micheli and Jordan, 2002). In fact, Micheli and Jordan provided mathematical proof that for a network with N unsynchronized sensors with sampling period T , the waiting time between two arrivals tends, in distribution, to the exponential random variable, that is $\delta_k \sim \mathcal{E}(\lambda)$, where $\lambda = N/T$, as N tends to infinity. In such cases, the expected value of the RV d_k is $E[d_k] = 1/\lambda$ and its variance is $\text{Var}[d_k] = 1/\lambda^2$.

3.3.5 Multi-Rate Sampling

The last irregularity discussed is the multi-rate sampling. Generally, it refers to multiple sensors measuring variables from the same system at different sampling rates. Figure 3.9 shows a schematic of causes and types of the multi-rate sampling irregularity.

Many industrial processes need to control variables that can be measured by online

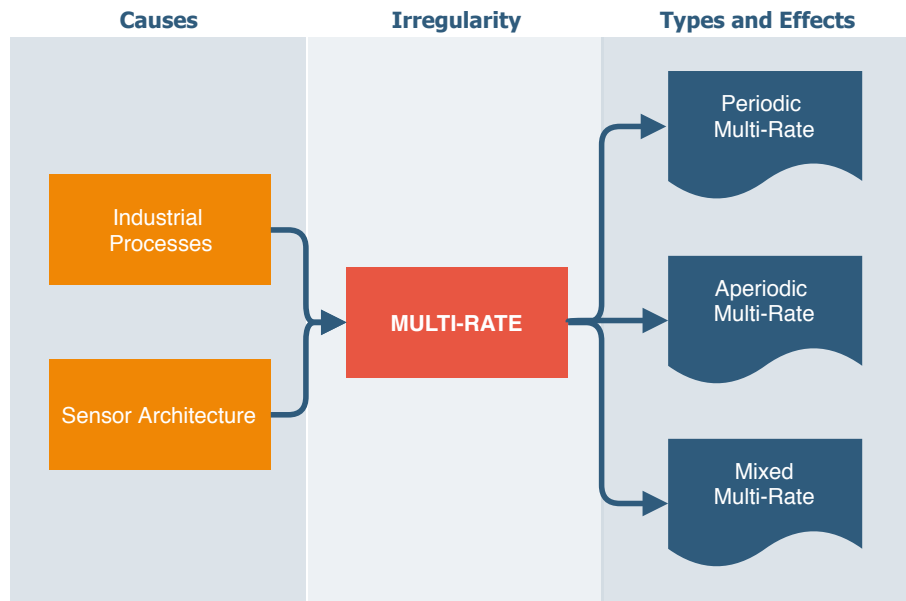


Figure 3.9: Multi-rate sampling diagram, showing the main causes (in orange) and types (in dark blue) of multi-rate sampling.

instruments that provide regular, fast rate and delay free information, but with low precision. Therefore, more accurate data are needed and usually available after slow, irregular and human-dependent laboratory analysis (Peñarrocha et al., 2012; Fatehi and Huang, 2017). The combination of both sources of measurements leads to a multi-rate sampling scenario.

A more common approach is the use of various sensors measuring the same physical information, to obtain better estimates, which has been drawing attention from real world applications, such as target tracking, robotics, surveillance and military. For such strategy, the sampling rates perceived by the estimator are often different from one another. The work of (Lin and Sun, 2016) and the references therein provide a wide coverage of scenarios derived from multi-sensor multi-rate systems.

Figure 3.10 illustrates the ways multi-rate sampling can be manifested in a system. The different rates from the various sensor devices can be periodic (a), aperiodic (b) or even a mixture of both, as it is the case for most industrial applications with laboratory analysis.

Aperiodic sampling rates can be described the same way as in Section 3.3.4, see (3.11). Periodic multi-rate measurements can be modeled as

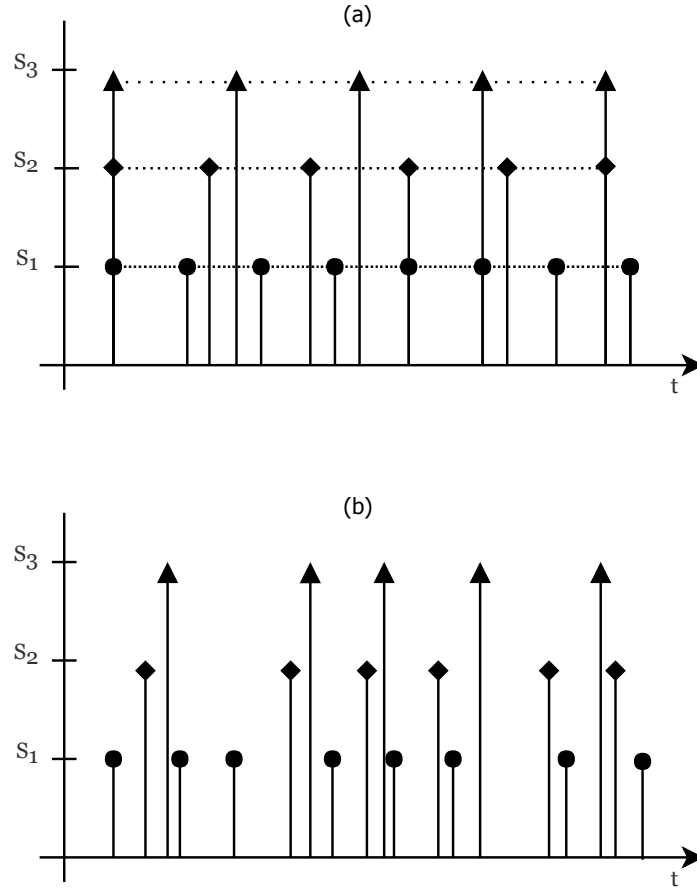


Figure 3.10: (a) Periodic and (b) aperiodic multi-rate sampling scheme. Labels S_1 , S_2 , S_3 refer to the sampling instants of three different sensors, from the highest sampling rate to the lowest sampling rate.

$$y_i(k_i T_i) = H_i(x(k_i T_i)) + v_i(k_i T_i) \quad (3.14)$$

where $y_i(k_i T_i)$ represents the k_i^{th} observation from sensor i with periodic sampling rate T_i and H_i is the discrete measurement model matrix related to that sensor.

3.4 Time Synchronization

There are techniques to handle all the irregularities discussed in this chapter and still achieve efficient state estimation performance. Provided that the estimator acknowledges the time that measurements were taken, there are many algorithms that provide interesting results. For some examples, we encourage the reader to check the

references from each subsection in this chapter.

In general, multi-sensor data fusion techniques for state estimation require that exact measurement time-stamps are available in order to assimilate data properly (Ping, 2003; Brahmi et al., 2013). However, that is not always the case and situations may arise in which time-stamps were not collected or their values are unreliable. Examples of the latter may occur when measurements are time stamped when they are received by the estimator instead of the moment it was taken, or when they are time stamped at local clocks without centralized synchronization (Julier and Uhlmann, 2005).

In many practical applications, if sampling irregularity cannot be accounted for accordingly, data are fused using the time of arrival as time-stamp (Huck et al., 2011), or irregularities such as OOSM are just disregarded completely (Kwok et al., 2004). The effects of such neglect has seldom been investigated, however. In one of the few studies, (Julier and Uhlmann, 2005) considered the state estimation problem for delayed but periodic observations with imprecise and unknown time-stamps, with the assumption that they could be statistically characterized. They proposed an implementation of the covariance union (CU) technique, using the time-stamp statistics in the filter update step. First, the method calculates the updates considering both the maximum and minimum expected delayed and then merged both results with a convex combination designed to minimize the state covariance matrix. CU algorithm was tested for the problem of estimating the states of a linear system, considering a random time delay, uniformly distributed between 2 and 10 time steps. Estimation performance was tested against four other methods: *known delay*, that considers the time delay to be known perfectly, as a baseline for comparison; *mean delay*, that assumes the delay to be always an average of 6 time steps; maximum likelihood, that calculates the likelihood of each possible time step and selects the highest; and Probabilistic Data Association Filter (PDAF) (Bar-shalom et al., 2009), that also calculates the likelihood of each step and averages the results using the likelihood as weight. They used the normalized state estimation error (NEES) test for consistency assessment, which we explain later in Section 4.4, for a linear system with two states. Therefore, the expected value of NEES for a consistent filter should be 2. The results are replicated in Table 3.1 for all algorithms.

As expected, the method with known delay was the most consistent, that is with $E[\text{NEES}]$ results closer to 2. CU and PDAF were both consistent, with slightly overestimated of the state error. They argued that, although PDAF obtained better consistency

Table 3.1: Comparison of NEES consistency test results for fusion of time delayed measurements with uncertain time-stamps for a linear system with two states

Method	E[NEES]
Known delay	1.9992
Mean delay	37.6949
Max likelihood	54.9323
Covariance union	1.3172
PDAF	1.8749

results, it has significantly higher computational costs. Nevertheless, the results of the mean delay and maximum likelihood are highly inconsistent, showing that the neglect or oversimplification of the imprecision in time-stamp leads to considerable performance degradation.

Another approach to overcome unknown time-stamps on the presence of sampling irregularities was studied by (Kwok et al., 2004). In the presence of OOSM, when sensor information is sampled at much faster rates than filter update rates, the real-time particle filter (RTPF) proposed by them, makes efficient use of all sensor information, instead of discarding sensor readings. That is achieved by dividing the received measurements among sample sets and then representing the states as a mixture of those sets.

Alternatively, in order to avoid performance degradation, one can make use of time synchronization schemes, widely used in communication networks, to ensure global time stamps. Wireless sensor networks (WSN) are particularly dependent on such techniques, due to limited computation, energy and communication resources of the sensing devices used. The work of (Sivrikaya and Yener, 2004) provide detailed reviews of the time synchronization problem in sensor networks. They explain the problem through computer clock mechanism.

With the aid of a hardware oscillator, local clocks from a sensing device node i approximates real time t as $C_i(t)$ by

$$C_i(t) = a_i t + b_i \quad (3.15)$$

where $a_i(t)$ is the clock *drift*, that is the clock frequency, and $b_i(t)$ represents an *offset* value, or the difference from real value t .

Clock approximations from two nodes in a network are compared by

$$C_1(t) = a_{12}C_2(t) + b_{12} \quad (3.16)$$

where a_{12} is the relative *drift* and b_{12} is the relative offset between nodes.

Under equations (3.15) and (3.16), the synchronization problem becomes the equalization of the computer clocks from all different n devices, in its most strict form. Thus, synchronization strategies can either match all clock frequencies and offsets once or perform repeated offset corrections over time. There are more relaxed versions of synchronizations, such as the one proposed by Römer (2003), that aims at maintaining only the order of events.

Probably the most popular time synchronization method is the one being used in the internet environment for years, the Network Time Protocol (NTP), designed by (Mills, 1991). For most control and WNS applications, however, it is not suitable, due to very different requirements, such as energy consumption, precision and scalability (Ganeriwal et al., 2003). An easy solution would be to equip all sensing devices in the network with a global positioning system (GPS) for a global time synchronization, but such solution is very expensive, not energy efficient and its signal might not work properly in every environment.

Therefore, many alternative methods have been proposed, and the work of (Kaur and Abhilasha, 2015) updates the studies from (Sivrikaya and Yener, 2004), with an exploration of the most recent synchronization protocols for sensor networks, that is: reference broadcast synchronization (RBS) (Elson et al., 2002); timing-sync protocol for sensor networks (TPSN) (Ganeriwal et al., 2003); delay measurement time synchronization (DMTS) (Ping, 2003); lightweight tree-based synchronization (LTS) (van Greunen and Rabaey, 2003); tiny-sync mini-sync (Sichitiu and Veerarittiphan, 2003); flooding time synchronization protocol (FTSP) (Maróti et al., 2004); lightweight and energy efficient time synchronization (LEETS) (Mingxia Xu et al., 2005); time diffusion protocol (TDP) (Su and Akyildiz, 2005); and time synchronization based on spanning tree (TSST) (He, 2008). A comparison adapted from Kaur and Abhilasha is presented in Table 3.2.

3.5 Chapter Summary and Final Remarks

In this chapter, the main sampling irregularities are reviewed: time delay, packet loss, uncertain observation, aperiodic and multi-rate. Diagrams describing their causes,

Table 3.2: Comparison of time synchronization methods. Parameters are *Precision*, *Energy Efficiency (E.E.)* and *Complexity (Comp.)*. Adapted from (Kaur and Abhilasha, 2015)

Protocol	Advantages	Limitations	Parameters
RBS	Eliminates random delays on the sender side	High amount of message exchanges and low transmission range	29.1 μs High E. E. High Comp.
TPSN	Eliminates the access, byte alignment and propagation times	Does not estimate the clock drift; does not handle dynamic topology changes and demands high communication load	16.9 μs High E. E. Low Comp.
DMTS	Reduces the number of message exchanges	Restricted to low resolution and low frequency external clocks	32 μs V. High E. E. Low Comp.
LTS	Robust and works well in the presence of dynamic links and fading.	The accuracy of synchronization decreases linearly in the depth of the synchronization tree	Unknown Low E. E. Low Comp.
Tiny-Sync Mini-Sync	Tolerant to message losses and adequate for networks with limited bandwidth and computational power	Unsuited for mobile sensor networks, high convergence time, not scalable and little robustness	945 μs High E. E. Low Comp.
FTSP	Robust, handles dynamic topology changes well and eliminates maximum delay components	Does not eliminate propagation delay and is not scalable	1.48 μs High E. E. High Comp.
LEETS	Low power consumption and low amount of message exchanges	Requires a GPS receiver in the root node	30 μs High E. E. Low Comp.
TDP	Tolerant to message losses, high mobility and performs well even without external servers	Very high convergence time	100 μs High E. E. High Comp.
TSST	Low synchronization error	Not scalable	Unknown Low E. E. Low Comp.

types and effects are shown for each of them. We also describe the necessary modifications to the observation models of state estimation algorithms. Most of the methods proposed in the literature to handle sampling irregularities rely on the correct time stamping of observations. Thus, time synchronization in sensor networks becomes crucial and its further explored. The most recent protocols developed to ensure a global time scale from sensing devices in large sensor networks are shown and compared.

However, the use of any time synchronization method will require computational, energy and resource consumption to some extent, apart from complex algorithms implementations. For sensor fusion performance applications in state estimation of sampled-data systems with irregular sampling, the investment might not be worth it. Thus, the next chapters try to shed some light in the evaluation of performance degradation in state estimation in the presence of irregular sampling, if time-stamps are not available.

State Estimation for Sampled-Data Systems

In this chapter, the field of sensor fusion under irregular sampling is resumed to the problem of estimating the states of a system with a known process model, that is observed by aperiodically sampled measurements. We begin by describing the discrete-time representation for sampled-data systems. Then we review the adopted state estimation algorithm, that is the Kalman Filter, which is the most common approach to probabilistic data fusion. The nonlinear extension based on the unscented transform is also explored. In Section 4.3 we describe the particularities of the filtering algorithms for when the correct time-stamp is available to the estimator and when it is not. We end with a description of the performance criteria used for assessment of the results, designed to quantify estimation accuracy and consistency.

4.1 Discrete-Time Representation of Sampled-Data Systems

State estimation methods introduced in this chapter are implementation for the discrete-time case. Therefore, the system described in Section 1.2 needs to be formulated as a discrete-time model. First, we reproduce the stochastic nonlinear sampled system models as follows

$$\dot{x}(t) = f(x(t), u(t), w(t), t), \quad (4.1)$$

$$y(t_k) = g(x(t_k), v(t_k), t_k), \quad (4.2)$$

where $f: \mathbb{R}^n \times \mathbb{R}^p \times \mathbb{R}^q \times \mathbb{R}^+ \rightarrow \mathbb{R}^n$ and $g: \mathbb{R}^n \times \mathbb{R}^r \times \mathbb{R}^+ \rightarrow \mathbb{R}^m$ are, respectively, the

process and observation models, $k \in \mathbb{N}$ is the discrete-time index, t_k represents the irregular time instants, $x(t) \in \mathbb{R}^n$ the state vector, $u(t) \in \mathbb{R}^p$ is the input vector and $w(t)$ is the process noise vector, all at continuous-time t , $y(t_k) \in \mathbb{R}^m$ represents the irregularly sampled measurement sequence and $v(t_k) \in \mathbb{R}^m$ the corresponding measurement noise vector. Initial condition x_0 is assumed to be known.

A continuous-time system dynamics defined by (4.1) can be discretized, by replacing the differentiation by differencing, via numerical methods. For this study we use the fourth order Runge-Kutta method (Süli and Mayers, 2003), where

$$x(t_{k+1}) = x(t_k) + \frac{1}{6} (k_1 + 2k_2 + 3k_3 + k_4), \quad (4.3)$$

$$t_{k+1} = t_k + h_k, \quad (4.4)$$

where $h_k \in \mathbb{R}$ is the variable step size, defined by random time intervals, and

$$k_1 = h_k f(t_k, x(t_k)), \quad (4.5)$$

$$k_2 = h_k f(t_k + \frac{h_k}{2}, x(t_k) + \frac{k_1}{2}), \quad (4.6)$$

$$k_3 = h_k f(t_k + \frac{h_k}{2}, x(t_k) + \frac{k_2}{2}), \quad (4.7)$$

$$k_4 = h_k f(t_k + h_k, x(t_k) + k_3), \quad (4.8)$$

where $f(x(t), u(t), w(t), t)$ was reduce to $f(x(t), t)$ for simplicity, since the numerical approximation depends only on the vector state itself and the time intervals. Input $u(t)$ is considered to be constant during the time step and $w(t)$ represents unknown noise. Therefore, the discrete-time representation for the nonlinear sampled system becomes

$$x(t_{k+1}) = f_d(x(t_k), u(t_k), w(t_k), t_k), \quad (4.9)$$

$$y(t_k) = g(x(t_k), v(t_k), t_k), \quad (4.10)$$

where $f_d(\cdot)$ is given by (4.3)-(4.8). Note that even if the nonlinear dynamics is time-invariant, that is $f(\cdot)$ does not depend directly on t_k , its discrete counterpart will be time-varying if the system is irregularly sampled, since there is a time-step dependent

factor outside $f(\cdot)$ for each k_n , $n = [1,2,3,4]$.

For the linear time-invariant case (LTI), the continuous state space representation is given by

$$\dot{x}(t) = Ax(t) + Bu(t) + w(t), \quad (4.11)$$

$$y(t_k) = Cx(t_k) + v(t_k), \quad (4.12)$$

where matrices $A \in \mathbb{R}^{n \times n}$, $B \in \mathbb{R}^{n \times p}$ and $C \in \mathbb{R}^{m \times n}$ are known matrices, $\rho(w(t)) = \mathcal{N}(0, Q)$ and $\rho(v(t_k)) = \mathcal{N}(0, R)$ are process and measurement noises, respectively, with covariance matrices $Q \in \mathbb{R}^{n \times q}$ and $R \in \mathbb{R}^{m \times r}$. If input $u(t)$ is digitally generated at the same rate than observations are taken, and followed by a digital-to-analog converter, then it is piecewise constant. That is, $u(t) = u(t_k)$, for $t_k \leq t < t_{k+1}$. In such cases, there is an exact solution to the discretization problem of (4.11), given by (Chen, 1999)

$$x(t_{k+1}) = A_d x(t_k) + B_d u(t_k) + w(t_k), \quad (4.13)$$

$$y(t_k) = C_d x(t_k) + v(t_k), \quad (4.14)$$

where $\rho(w(t_k)) = \mathcal{N}(0, Q_d)$ and subscript d is short for *discretized*. The matrices from the discrete-time representation are given by

$$A_d = e^{Ah_k}, \quad (4.15)$$

$$B_d = \left(\int_{\tau=t_k}^{t_{k+1}} e^{A\tau} \delta\tau \right) B, \quad (4.16)$$

$$C_d = C, \quad (4.17)$$

$$Q_d = \int_{\tau=t_k}^{t_{k+1}} e^{A\tau} Q e^{A^T \tau} \delta\tau, \quad (4.18)$$

where $h_k = t_{k+1} - t_k \in \mathbb{R}$ as in (4.4), is the variable step size, defined by the random time intervals. Note that, once again, even for the time-invariant case, the matrices from the discrete-time system depend on time intervals, thus will be time-variant if they vary throughout time.

Usually, the covariance matrices Q and R of the noise vectors, that represent the

noise level, are better expressed by a signal-to-noise ratio (SNR) quantity, which is a more directly related measure to how contaminated is a signal. It is basically a relation between the power level of the signal and of the noise, that is

$$SNR = \frac{P_{\text{signal}}}{P_{\text{noise}}}, \quad (4.19)$$

where P is the average power of a signal, which is directly proportional to its variance. Therefore it can also be expressed by

$$SNR = \frac{\sigma_{\text{signal}}^2}{\sigma_{\text{noise}}^2}. \quad (4.20)$$

In Chapter 5 we use SNR definition to express the noise level present in signals, using the logarithmic decibel (dB) scale, given by

$$SNR_{\text{dB}} = 10 \log_{10} \frac{P_{\text{signal}}}{P_{\text{noise}}}, \quad (4.21)$$

In the next section we introduce the estimation problem and the Bayesian solution, considering the discrete-time models of state space representations. For simplicity, we replace (t_k) argument for a subscript k , to represent discrete instants of time.

4.2 Bayesian Estimation

The Bayesian approach to state estimation can be interpreted as a data fusion algorithm in which the inferred knowledge about the system's states is updated as new information arrives, using not just the new data, but also the prior information. For that, both the states and the arrived information are modeled as random variables (RV), hence its classification falls under the probabilistic fusion framework.

The goal of the estimator is to statistically and recursively infer the values of the system's states, that is the random vector $x_k \in \mathbb{R}^n$, from noisy data, that is the observation vector sequence $y_1, \dots, y_k \in \mathbb{R}^m$ and input vector sequence $u_1, \dots, u_k \in \mathbb{R}^p$. The corresponding conditional PDF, $\rho(x_k | (y_1, \dots, y_k))$, is called the *posterior* PDF, describing the statistics of the random vector $x_k \in \mathbb{R}^n$, after the present and past experimental observations $\rho(x_k | (y_1, \dots, y_k))$ have been assimilated and the process model has been taken into account. Thus we can find the estimation of x_k using methods such as the *maximum*

a posteriori (MAP) or *minimum mean square error* (MMSE), given by (Bar-Shalom et al., 2001)

$$\hat{x}_k^{MAP} \triangleq \arg \max_{x_k} \hat{\rho}(x_k | (y_1, \dots, y_k)), \quad (4.22)$$

$$\hat{x}_k^{MMSE} \triangleq \arg \min_{x_k} E[(\hat{x}_k - x_k)^T (\hat{x}_k - x_k) | (y_1, \dots, y_k)], \quad (4.23)$$

where \hat{x}_k is the estimated value of $x_k \in \mathbb{R}^n$, $\hat{\rho}(x_k | (y_1, \dots, y_k))$ is the estimated posterior PDF of x_k given the observation sequence, and $E[(\hat{x}_k - x_k)^T (\hat{x}_k - x_k) | (y_1, \dots, y_k)]$ is the variance of the random vector x_k , given the observation sequence. MAP can be interpreted as the bayesian approach to *maximum likelihood* (ML) estimation, whereas MMSE is the counterpart of the *least squares* (LS) estimator (Bar-Shalom et al., 2001).

Finding the *posterior* $\rho(x_k | (y_1, \dots, y_k))$ defines the complete state estimation problem, whereas the estimates $\hat{x}_k^{MAP} \in \mathbb{R}^n$ and $\hat{x}_k^{MMSE} \in \mathbb{R}^n$ are the optimal state estimates, under their optimality criteria. A recursive Bayesian solution to the state estimation problem, that is finding the *posterior* PDF, considering that the system evolves according a Markov process is presented in Proposition 4.2.1. But first, we need to define two lemmas.

Lemma 4.2.1. For a Markov system with initial state $x_0 \sim \rho(x_0)$, the transition PDF of the future state x_{k+1} given the present state x_k is independent of past states, that is

$$\rho(x_{k+1} | (x_0, \dots, x_k)) = \rho(x_{k+1} | x_k), \quad (4.24)$$

and observation vector y_k is independent of past observations and past states, given the present state x_k , that is

$$\rho(y_k | (x_0, \dots, x_k, y_0, \dots, y_{k-1})) = \rho(y_k | x_k). \quad (4.25)$$

Lemma 4.2.2. For a Markov system, we can find the transition PDF from step n to step s as a function of the transition densities between them and an intermediate step r , as long as $n > r > s$, by the Chapman-Kolmogorov equation (Papoulis, 1984)

$$\rho(x_n | x_s) = \int_{-\infty}^{\infty} \rho(x_n | x_r) \rho(x_r | x_s) dx_r. \quad (4.26)$$

Note that the systems described in Section 4.1 are Markovian, since the transition or process models given by (4.9) and (4.13) and the observation models given by (4.10) and (4.14) follow the conditions (4.24) and (4.25), respectively.

Proposition 4.2.1. The posterior PDF of system states $x_k \in \mathbb{R}^n$ conditioned on the observation vector sequence $y_1, \dots, y_k \in \mathbb{R}^m$ is recursively given by

$$\rho(x_k|y_1, \dots, y_{k-1}) = \int_{\mathbb{R}^n} \rho(x_k|x_{k-1})\rho(x_{k-1}|y_1, \dots, y_{k-1})dx_{k-1}, \quad (4.27)$$

$$\rho(x_k|y_1, \dots, y_k) = \frac{\rho(y_k|x_k)\rho(x_k|y_1, \dots, y_{k-1})}{\rho(y_k|y_1, \dots, y_{k-1})} \quad (4.28)$$

where $k \in \mathbb{N}$, $\rho(y_k|x_k)$ is the *likelihood PDF*, $\rho(x_k|y_1, \dots, y_{k-1})$ is the *prior PDF*, defined before the latest measurement, $\rho(x_k|x_{k-1})$ is the *transition PDF* that models the evolution of x_k and $\rho(y_k|y_1, \dots, y_{k-1})$ is the *evidence*, also referred to as normalizing factor, or marginalization.

Proof. The posterior PDF can be computed by the *Bayes' rule* (Stone, 2013)

$$\rho(x_k|y_1, \dots, y_k) = \frac{\rho((y_1, \dots, y_k)|x_k)\rho(x_k)}{\rho(y_1, \dots, y_k)}. \quad (4.29)$$

Using the definition of the conditional probability, given by (Papoulis, 1984)

$$\rho((a_1, \dots, a_k)|(a_{k+1}, \dots, a_n)) = \frac{\rho(a_1, \dots, a_k, \dots, a_n)}{\rho(a_{k+1}, \dots, a_n)}, \quad (4.30)$$

and the chain rule of probability, that is (Papoulis, 1984)

$$\rho(a_1, \dots, a_n) = \rho(a_n|a_1, \dots, a_{n-1})\rho(a_1, \dots, a_{n-1}), \quad (4.31)$$

it is possible to rewrite (4.29) as

$$\rho(x_k|y_1, \dots, y_k) = \frac{\rho(y_k|y_1, \dots, y_{k-1}, x_k)\rho(y_1, \dots, y_{k-1}|x_k)\rho(x_k)}{\rho(y_k|y_1, \dots, y_{k-1})\rho(y_1, \dots, y_{k-1})}. \quad (4.32)$$

From Lemma 4.2.1, given the current state x_k , the present y_k is independent of past observations, thus the first term of the dividend becomes $\rho(y_k|x_k)$. Additionally, Bayes' rule in the second term yields

$$\rho((y_1, \dots, y_{k-1})|x_k) = \frac{\rho(x_k|(y_1, \dots, y_{k-1}))\rho((y_1, \dots, y_{k-1}))}{\rho(x_k)}. \quad (4.33)$$

Finally, by combining all together, we have

$$\rho(x_k|(y_1, \dots, y_k)) = \frac{\rho(y_k|x_k)\rho(x_k|(y_1, \dots, y_{k-1}))\rho((y_1, \dots, y_{k-1}))\rho(x_k)}{\rho(y_k|(y_1, \dots, y_{k-1}))\rho(y_1, \dots, y_{k-1})\rho(x_k)}, \quad (4.34)$$

which, after canceling the equal terms (in gray), proves (4.28).

To prove (4.27), we introduce a predicted state x_{k+1} in the posterior PDF, that is $\rho(x_{k+1}, x_k|(y_1, \dots, y_k))$ (Bergman, 1999). Rewriting the new conditional PDF with the aid of (4.30), (4.31) and Lemma 4.2.1, we have

$$\begin{aligned} \rho(x_{k+1}, x_k|(y_1, \dots, y_k)) &= \rho(x_{k+1}|(x_k, y_1, \dots, y_k))\rho(x_k|(y_1, \dots, y_k)) \\ &= \rho(x_{k+1}|(x_k))\rho(x_k|(y_1, \dots, y_k)). \end{aligned} \quad (4.35)$$

The integration of both sides of (4.35) with respect to x_k yields (4.27), which is also a Chapman-Kolmogorov equation. This last piece of proof is also an application of Lemma 4.2.2.

□

The evidence term in the denominator of (4.28) is commonly presented as a constant (Särkkä, 2013), since it does not depend on the state vector x_k , and it can be computed by the Chapman-Kolmogorov equation from Lemma 4.2.2

$$\begin{aligned} \rho(y_k|(y_1, \dots, y_{k-1})) &= \int_{\mathbb{R}^n} \rho(y_k|x_k)\rho(x_k|(y_1, \dots, y_{k-1}))dx_k, \\ &= z_k. \end{aligned} \quad (4.36)$$

The algorithm is initialized by a known prior $\rho(x_0)$ and recursion is achieved by introducing the PDF calculated in the *forecast* step, given by (4.27), in the *data assimilation* step, given by (4.28). Thus, (4.28) can be interpreted as the fusion of the *prior* PDF or knowledge of the state with the *likelihood* PDF or evidence. For a better understanding, we can illustrate this process for a one-dimensional Gaussian case (Faragher, 2012), for which the PDFs are given by

$$\begin{aligned}\rho(x_k|y_1, \dots, y_{k-1}) &= \mathcal{N}(x_k|\hat{x}_p, \hat{\sigma}_p) \\ &= \frac{1}{\sqrt{2\pi}\hat{\sigma}_p} \exp\left(-\frac{(x_k - \hat{x}_p)^2}{2\hat{\sigma}_p^2}\right),\end{aligned}\quad (4.37)$$

$$\begin{aligned}\rho(y_k|x_k) &= \mathcal{N}(y_k|x_k, \hat{\sigma}_e) \\ &= \frac{1}{\sqrt{2\pi}\hat{\sigma}_e} \exp\left(-\frac{(y_k - x_k)^2}{2\hat{\sigma}_e^2}\right),\end{aligned}\quad (4.38)$$

where the subscript p stands for *prior* and the subscript e stands for *evidence*. The *prior* PDF defined in (4.37) is obtained by forecasting with the aid of a process model, and the *likelihood* PDF given by (4.38) is obtained by a linear observation model, say $y_k = x_k + w_k$, with $w_k \sim \mathcal{N}(0, \sigma_e)$. Under the MAP estimation method, we can combine (4.22) and (4.28), discarding the normalization factor, which is independent of x_k , yielding

$$\begin{aligned}\hat{x}_k^{MAP} &= \arg \max_{x_k} \rho(y_k|x_k) \rho(x_k|y_1, \dots, y_{k-1}) \\ &= \arg \max_{x_k} \mathcal{N}(y_k|x_k, \hat{\sigma}_e) \mathcal{N}(x_k|\hat{x}_p, \hat{\sigma}_p),\end{aligned}\quad (4.39)$$

and from the multiplication of (4.37) and (4.38) we have that

$$\begin{aligned}\mathcal{N}(y_k|x_k, \hat{\sigma}_e) \mathcal{N}(x_k|\hat{x}_p, \hat{\sigma}_p) &= \frac{1}{\sqrt{2\pi}\hat{\sigma}_p} \exp\left(-\frac{(x_k - \hat{x}_p)^2}{2\hat{\sigma}_p^2}\right) \times \frac{1}{\sqrt{2\pi}\hat{\sigma}_e} \exp\left(-\frac{(y_k - x_k)^2}{2\hat{\sigma}_e^2}\right) \\ &= \frac{1}{2\pi\hat{\sigma}_p\hat{\sigma}_e} \exp\left[-\left(\frac{(y_k - x_k)^2}{2\hat{\sigma}_e^2} + \frac{(x_k - \hat{x}_p)^2}{2\hat{\sigma}_p^2}\right)\right],\end{aligned}\quad (4.40)$$

whose quadratic terms can be expanded and, apart from a constant term that will be handled by the normalization factor discarded in 4.39, is rearranged into

$$\begin{aligned}\mathcal{N}(y_k|x_k, \hat{\sigma}_e) \mathcal{N}(x_k|\hat{x}_p, \hat{\sigma}_p) &= \mathcal{N}(x_k|\mu_{\text{fused}}(y_k), \hat{\sigma}_{\text{fused}}) \\ &= \frac{1}{\sqrt{2\pi}\hat{\sigma}_{\text{fused}}} \exp\left(-\frac{(x_k - \mu_{\text{fused}}(y_k))^2}{2\hat{\sigma}_{\text{fused}}^2}\right),\end{aligned}\quad (4.41)$$

where

$$\begin{aligned}\mu_{\text{fused}}(y_k) &\triangleq \hat{x}_{\text{posterior}}(y_k) = \frac{\hat{\sigma}_e^2}{\hat{\sigma}_p^2 + \hat{\sigma}_e^2} \hat{x}_p + \frac{\hat{\sigma}_p^2}{\hat{\sigma}_e^2 + \hat{\sigma}_p^2} y_k \\ &= \hat{x}_p + \frac{\hat{\sigma}_p^2}{\hat{\sigma}_e^2 + \hat{\sigma}_p^2} (y_k - \hat{x}_p),\end{aligned}\quad (4.42)$$

$$\begin{aligned}\hat{\sigma}_{\text{fused}} &\triangleq \hat{\sigma}_{\text{posterior}} = \frac{\hat{\sigma}_p^2 \hat{\sigma}_e^2}{\hat{\sigma}_p^2 + \hat{\sigma}_e^2} \\ &= \hat{\sigma}_p^2 - \frac{\hat{\sigma}_p^2}{\hat{\sigma}_e^2 + \hat{\sigma}_p^2} \hat{\sigma}_p^2.\end{aligned}\quad (4.43)$$

The derivation from (4.42) and (4.43) comes from the multiplication of two Gaussian PDFs. Combining the results of (4.42) and (4.43) with (4.39), we have that

$$\begin{aligned}\hat{x}_k^{\text{MAP}} &= \arg \max_{x_k} \mathcal{N}(x_k | \hat{x}_{\text{posterior}}(y_k), \hat{\sigma}_{\text{posterior}}) \\ &= \hat{x}_{\text{posterior}}(y_k).\end{aligned}\quad (4.44)$$

In other words, the MAP estimate will be the mean of the *posterior* Gaussian, with its new parameters determined by a weighted combination of the variances of both *prior* and *likelihood* PDFs. The information that holds the lowest uncertainty will be favored. Figure 4.1 presents the result of two fusions, each with a different Gaussian density being the most certain one.

4.2.1 Kalman Filter

The Bayesian recursive solution described by Proposition 4.2.1 enables the computation of the optimal estimation of state vector x_k . However, its implementation is impossible for practical applications, since it relies on mathematical integrations and as time evolves, the observation sequence grows indefinitely. The sequential algorithm proposed by (Kalman, 1960) solves that problem adding a restriction in the system assumptions, that is linearity and Gaussianity.

Consider the Gauss-Markov discrete-time linear system

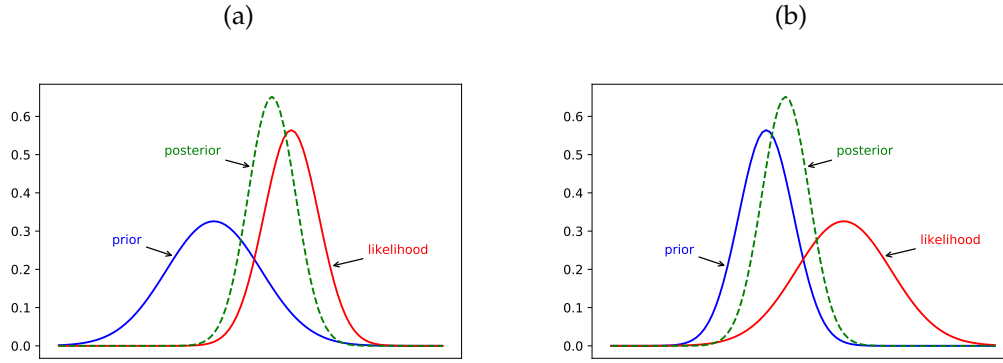


Figure 4.1: *Posterior* PDF obtained by the fusion of *prior* and *likelihood* densities. In (a) the variance of the *likelihood* is smaller than the variance of the *prior*, hence the *posterior* is closer to the *likelihood*. In (b) is the other way around.

$$x_k = A_{k-1}x_{k-1} + B_{k-1}u_{k-1} + G_{k-1}w_{k-1}, \quad (4.45)$$

$$y_k = C_k x_k + v_k, \quad (4.46)$$

where, $\forall k \geq 1$, time varying matrices $A_{k-1} \in \mathbb{R}^{n \times n}$, $B_{k-1} \in \mathbb{R}^{n \times p}$, $G_{k-1} \in \mathbb{R}^{n \times q}$ and $C_{k-1} \in \mathbb{R}^{m \times n}$ are known, as well as the input $u_{k-1} \in \mathbb{R}^p$ and output $y_k \in \mathbb{R}^m$ vectors. Process and observation noise vectors, $w_{k-1} \in \mathbb{R}^q$ and $v_{k-1} \in \mathbb{R}^m$ are white, zero-mean and mutually independent, apart from being Gaussian, with known covariance matrices Q_{k-1} and R_k , respectively.

Define $\mathcal{N}(x; \bar{x}, P^{xx})$ as a multivariate Gaussian PDF on x , with mean \bar{x} and covariance P^{xx} , given by

$$\mathcal{N}(x; \mu, P^{xx}) \triangleq \frac{1}{(2\pi)^{n/2} |P^{xx}|^{1/2}} \exp\left(-\frac{1}{2}(x - \mu)^T (P^{xx})^{-1} (x - \mu)\right) \quad (4.47)$$

Some identities of multivariate Gaussian probability densities are needed for the next steps and are described in properties 4.2.1 and 4.2.2.

Property 4.2.1. If the random variables x and y are Gaussian RVs,

$$\rho(x, y) = \mathcal{N}\left(\begin{pmatrix} x \\ y \end{pmatrix}; \begin{pmatrix} a \\ b \end{pmatrix}, \begin{pmatrix} A & C \\ C^T & B \end{pmatrix}\right) \quad (4.48)$$

then, the marginal and conditional PDFs of x and y are given by

$$\rho(x) = \mathcal{N}(x; a, A) \quad (4.49)$$

$$\rho(y) = \mathcal{N}(y; b, B) \quad (4.50)$$

$$\rho(x|y) = \mathcal{N}(x; a + CB^{-1}(y - b), A - CB^{-1}C^T) \quad (4.51)$$

$$\rho(y|x) = \mathcal{N}(y; b + C^T A^{-1}(x - a), B - C^T A^{-1}C) \quad (4.52)$$

Property 4.2.2. If x and y are Gaussian RVs, with PDFs given by

$$\rho(x) = \mathcal{N}(x; a, A), \quad (4.53)$$

$$\rho(y|x) = \mathcal{N}(y; Hx, B), \quad (4.54)$$

then, the joint and marginal PDFs are defined by

$$\rho(x, y) = \mathcal{N}\left(\begin{pmatrix} x \\ y \end{pmatrix}; \begin{pmatrix} a \\ Ha \end{pmatrix}, \begin{pmatrix} A & AH^T \\ HA & HAH^T + B \end{pmatrix}\right), \quad (4.55)$$

$$\rho(y) = \mathcal{N}(y; Ha, HAH^T + B) \quad (4.56)$$

From the Gauss-Markov assumptions, we can rewrite (4.45) and (4.46) from a probabilistic perspective, as

$$\rho(x_k|x_{k-1}) = \mathcal{N}(x_k; A_{k-1}\bar{x}_{k-1} + B_{k-1}u_{k-1}, Q_k), \quad (4.57)$$

$$\rho(y_k|x_k) = \mathcal{N}(y_k; C_k\bar{x}_k, R_k), \quad (4.58)$$

where (4.57) is the *transition* density representing the system dynamics and (4.58) is the *likelihood* density, given by the observation model.

The Bayesian recursive solution to such system is defined by *forecast* and *data assimilation* steps according to

$$\rho(x_k|y_1, \dots, y_{k-1}) = \mathcal{N}(x_k; \hat{x}_{k|k-1}, P_{k|k-1}^{xx}), \quad (4.59)$$

$$\rho(x_k|y_1, \dots, y_k) = \mathcal{N}(x_k; \hat{x}_{k|k}, P_{k|k}^{xx}), \quad (4.60)$$

with the *posterior* density function from a previous step given by

$$\rho(x_{k-1}|y_1, \dots, y_{k-1}) = \mathcal{N}(x_{k-1}; \hat{x}_{k-1|k-1}, P_{k-1|k-1}^{xx}), \quad (4.61)$$

where $\hat{x}_{k|k-1}$ and $P_{k|k-1}^{xx}$ are the *forecast* state and covariance estimates, whereas $\hat{x}_{k|k}$ and $P_{k|k}^{xx}$ are the *data assimilation* state and covariance estimates.

Now we combine the *forecast steps* from (4.27) and from (4.59), using the process model from (4.57), the previous estimate from (4.61) and the identities from property 4.2.2, yielding

$$\begin{aligned} \rho(x_k|y_1, \dots, y_{k-1}) &= \int_{\mathbb{R}^n} \rho(x_k|x_{k-1})\rho(x_{k-1}|y_1, \dots, y_{k-1})dx_{k-1}, \\ &= \mathcal{N}(x_k; A_{k-1}\hat{x}_{k-1|k-1} + B_{k-1}u_{k-1}, A_{k-1}P_{k-1|k-1}^{xx}Ak - 1^T + G_{k-1}QG_{k-1}^T), \end{aligned} \quad (4.62)$$

that is, the *forecast* state and covariance estimates are computed by

$$\hat{x}_{k|k-1} = A_{k-1}\hat{x}_{k-1|k-1} + B_{k-1}u_{k-1}, \quad (4.63)$$

$$P_{k|k-1}^{xx} = A_{k-1}P_{k-1|k-1}^{xx}A_{k-1}^T + G_{k-1}QG_{k-1}^T. \quad (4.64)$$

And for the *data assimilation step*, we find the joint density of y_k with the *forecast* estimate from (4.62), using property 4.2.1

$$\rho(x_k, y_k|y_1, \dots, y_{k-1}) = \mathcal{N}\left(\begin{pmatrix} x_k \\ y_k \end{pmatrix}; \begin{pmatrix} \hat{x}_{k|k-1} \\ C_k \hat{x}_{k|k-1} \end{pmatrix}, \begin{pmatrix} P_{k|k-1}^{xx} & P_{k|k-1}^{xx} C_k^T \\ C_k P_{k|k-1}^{xx} & C_k P_{k|k-1}^{xx} C_k^T + R_k \end{pmatrix}\right), \quad (4.65)$$

and the marginal density for x_k is

$$\rho(x_k | (y_1, \dots, y_k)) = \mathcal{N}(x_k; \hat{x}_{k|k-1} + K_k(y_k - C_k \hat{x}_{k|k-1}), P_{k|k-1}^{xx} - P_{k|k-1}^{xx} C_k^T K_k^{-1} P_{k|k-1}^{xx} C_k^T), \quad (4.66)$$

that is, the *data assimilation* state and covariance estimates are calculated by

$$\hat{x}_{k|k} = \hat{x}_{k|k-1} + K_k(y_k - C_k \hat{x}_{k|k-1}), \quad (4.67)$$

$$P_{k|k}^{xx} = P_{k|k-1}^{xx} - P_{k|k-1}^{xx} C_k^T K_k^{-1} P_{k|k-1}^{xx} C_k^T. \quad (4.68)$$

where $K_k \in \mathbb{R}^{n \times m}$ is defined as the Kalman gain and is given by

$$K_k = P_{k|k-1}^{xx} C_k^T (C_k P_{k|k-1}^{xx} C_k^T + R_k)^{-1}. \quad (4.69)$$

If we define a *forecast* output estimate $\hat{y}_{k|k-1}$, an innovation covariance matrix $P_{k|k-1}^{yy}$ and a cross-covariance matrix $P_{k|k-1}^{xy}$ as

$$\hat{y}_{k|k-1} \triangleq C_k \hat{x}_{k|k-1}, \quad (4.70)$$

$$P_{k|k-1}^{yy} \triangleq E[(y_k - \hat{y}_{k|k-1})(y_k - \hat{y}_{k|k-1})^T] = C_k P_{k|k-1}^{xx} C_k^T + R_k, \quad (4.71)$$

$$P_{k|k-1}^{xy} \triangleq E[(x_k - \hat{x}_{k|k-1})(y_k - \hat{y}_{k|k-1})^T] = P_{k|k-1}^{xx} C_k^T, \quad (4.72)$$

$$(4.73)$$

we can simplify *data assimilation* step given by (4.67), (4.68) and (4.69) as

$$\hat{x}_{k|k} = \hat{x}_{k|k-1} + K_k(y_k - \hat{y}_{k|k-1}), \quad (4.74)$$

$$P_{k|k}^{xx} = P_{k|k-1}^{xx} - P_{k|k-1}^{xy} K_k^{-1} (P_{k|k-1}^{yy})^T, \quad (4.75)$$

$$K_k = P_{k|k-1}^{xy} (P_{k|k-1}^{yy})^{-1}. \quad (4.76)$$

For more details on this derivation, refer to (Särkkä, 2013). We summarize the Kalman filter algorithm as below

Algorithm 4.2.1. Kalman filter (KF) algorithm.

Forecast step: Using the linear model, calculate the estimated state vector

$\hat{x}_{k|k-1}$ and the estimated state covariance $P_{k|k-1}^{xx}$, using (4.63) and (4.64). Calculate Kalman gain K_k by (4.69).

Data assimilation step: Using the measurement vector y_k and Kalman gain, update estimations from previous step with (4.67) and (4.68), obtaining estimates $\hat{x}_{k|k}$ and $P_{k|k}^{xx}$.

The linear KF is the optimal estimator under both MAP and MMSE criteria, it is unbiased and its cross-covariance will asymptotically achieve the lower bound of the Cramér-Rao inequality (Teixeira, 2008).

4.2.2 Unscented Kalman Filter

For nonlinear systems, the Gaussianity requirement does not hold, even if the uncertainty and initial conditions are Gaussian. Therefore, we can not characterize the posterior PDF only by its first two moments, mean and covariance, and the solution given by proposition 4.2.1 are not suited for the estimation problem. In fact, optimal solutions are generally not possible to be obtained by a recursive algorithm.

Adaptations to the Kalman filter have been proposed in the literature. The extended Kalman filter (EKF), for example, linearizes the system around the current state estimates, to achieve approximations using Algorithm 4.2.1. A different approach is to approximate the statistics of the posterior PDF, instead of the model. The unscented Kalman filter (UKF) (Julier and Uhlmann, 2004) performs statistical approximations via the unscented transform (UT), based on the Monte Carlo approach.

First, we define a set of samples $\chi \triangleq [\chi_1, \dots, \chi_{2n}] \in \mathbb{R}^{n \times 2n}$, also referred to as sigma points, to estimate the mean \bar{x} and covariance \bar{P}^{xx} of the random variable being approximated, such that

$$\sum_{i=0}^{2n} \gamma_i \chi_i = \bar{x}, \quad (4.77)$$

$$\sum_{i=0}^{2n} \gamma_i [(\chi_i - \bar{x})(\chi_i - \bar{x})^T] = \bar{P}^{xx}, \quad (4.78)$$

$$\sum_{i=0}^{2n} \gamma_i = 1. \quad (4.79)$$

where $\gamma_i, \forall i > 1$ are called weights. There are various ways of determining the sigma points, but we choose a simplified version of the original UT proposed by (Julier and Uhlmann, 1997), which each χ_i is given by a column of the matrix $\chi = [\chi_1 \chi_2 \dots \chi_{2n}]$ given by

$$\chi \triangleq \begin{bmatrix} \bar{x}1_{1 \times 2n} + \sqrt{n}(\bar{P}^{xx})^{1/2} & \bar{x}1_{1 \times 2n} - \sqrt{n}(\bar{P}^{xx})^{1/2} \end{bmatrix}, \quad (4.80)$$

with weights

$$\gamma' = \frac{1}{2n}. \quad (4.81)$$

Such simplification has one less tuning degree of freedom to approximate higher order moments of the RV, called scaling factor. We now define the UT algorithm as follows

Algorithm 4.2.2. Unscented Transform (UT) algorithm

Consider a nonlinear transformation of two random variables y and x

$$y = f(x, d), \quad (4.82)$$

where x has mean $\bar{x} \in \mathbb{R}^n$ and covariance matrix $P^{xx} \in R^{n \times n}$ and d is a deterministic vector. First, compute sigma points matrix χ and its correspondent weights γ according to (4.80) and (4.81) respectively. Propagate each sigma point χ_i through the nonlinear transformation given by (4.82) to find estimated mean \hat{y} and covariance matrix P^{yy} of the RV y and the cross-covariance matrix P^{xy} , by

$$\Upsilon_i = f(\chi_i, d), \quad \forall i = 1, \dots, 2n \quad (4.83)$$

$$\hat{y} = \sum_{i=0}^{2n} \gamma_i \Upsilon_i, \quad (4.84)$$

$$P^{yy} = \sum_{i=0}^{2n} \gamma_i [(\Upsilon_i - \hat{y})(\Upsilon_i - \hat{y})^T], \quad (4.85)$$

$$P^{xy} = \sum_{i=0}^{2n} \gamma_i [(\Upsilon_i - \hat{y})(\chi_i - \bar{x})^T]. \quad (4.86)$$

For simplicity, we will refer to (4.83-4.86) as the function ψ_{UT} , given by

$$[\hat{y} \ P^{yy} \ P^{xy}] = \psi_{UT}(\bar{x}, P^{xx}, n, d, f) \quad (4.87)$$

Based on Algorithm 4.2.2, and considering the process and observation models given by (1.1) and (1.2), the UKF algorithm is as follows

Algorithm 4.2.3. Unscented Kalman filter (UKF) algorithm.

Forecast step: Use the UT to calculate the forecast state estimate $\hat{x}_{k|k-1}$ and the respective covariance $P_{k|k-1}^{xx}$ based on last estimation

$$\begin{bmatrix} \hat{x}_{k|k-1} & P_{k|k-1}^{xx} \end{bmatrix} = \psi_{UT}(\hat{x}_{k-1|k-1}, P_{k-1|k-1}^{xx}, n, d, f), \quad (4.88)$$

where f is given by (1.1) and d by current input data and time instant.

Based on forecast state estimate and covariance found in (4.88), compute the forecast observation estimate $\hat{y}_{k|k-1}$, observation vector covariance $P_{k|k-1}^{yy}$ and the cross-covariance between observation and state $P_{k|k-1}^{xy}$, via the UT

$$\begin{bmatrix} \hat{y}_{k|k-1} & P_{k|k-1}^{yy} & P_{k|k-1}^{xy} \end{bmatrix} = \psi_{UT}(\hat{x}_{k|k-1}, P_{k|k-1}^{xx}, n, d, g), \quad (4.89)$$

where g is given by (1.2) and d by current time instant.

Data assimilation step: Calculate Kalman gain and current state estimate and covariance at time k , same way as in (4.74-4.76), reproduced for convenience

$$K_k = P_{k|k-1}^{xy} (P_{k|k-1}^{yy})^{-1}, \quad (4.90)$$

$$\hat{x}_{k|k} = \hat{x}_{k|k-1} + K_k (y_k - \hat{y}_{k|k-1}), \quad (4.91)$$

$$P_{k|k}^{xx} = P_{k|k-1}^{xx} - P_{k|k-1}^{xy} K_k^{-1} (P_{k|k-1}^{yy})^T. \quad (4.92)$$

UKF algorithm addresses many of the drawbacks that appear in the EKF implementation, such as the necessity of differentiability, the performance loss due to systems that are poorly approximated by linearization and computational efficiency. Therefore the UKF is the chosen method for the nonlinear system simulated in Chapter 5 and will be further discussed in this section.

4.3 State Estimation with Aperiodic Sampling

The exact solution to the linear discretization problem, defined by (4.13) and (4.14) considered digital inputs sampled at the same rate as the observations were taken, producing a sequence of data at time instants $t_k, \forall k \in \mathbb{N}$. The nonlinear solution is agnostic to this assumption, since it relies on numerical approximations. Nevertheless, the representation given by (4.9) and (4.10) is constructed using a common time sequence $t_k, \forall k \in \mathbb{N}$ for both process and observation models.

However, we are interested in the effects of aperiodic sampling of the observations and data assimilation executed at incorrect time instants, as formulated in Section 1.2. For that, we consider that input signal $u(t)$ is generated by a digital device using an *ideal sampler*, with a regular time interval T , that is $u(t) = u(iT)$, for $iT \leq t < (i+1)T, \forall i \in \mathbb{N}$. Estimation time instants needs to coincide with the regularly spaced time intervals T . Measurement instants $t_k, \forall k \in \mathbb{N}$ do not match the estimation instants $iT, \forall i \in \mathbb{N}$. Additionally, input data $u(iT)$ is available a rate $1/T$ that is $\alpha > 1$ times faster than the expected sampling rate λ_h of the observations. An illustrative example is presented in Figure 4.2, where $\alpha = 5$, that is the expected time interval for observations $1/\lambda_h$ is five times higher than regular sampling time interval T .

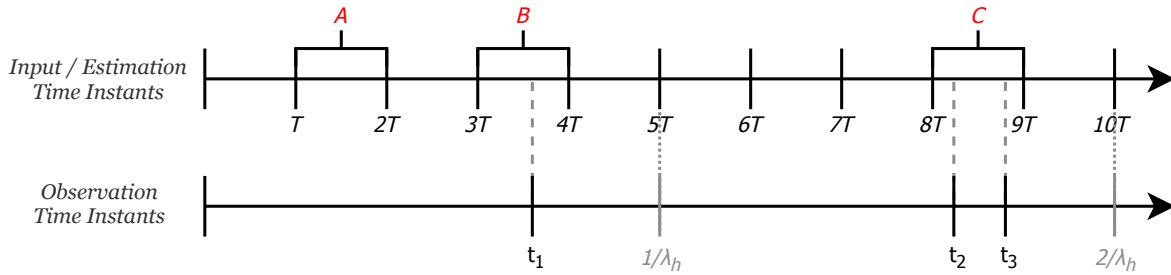


Figure 4.2: Input and estimation time instants labeled as iT and a realization of observation time instants, labeled as t_k . Expected time instants for observation is presented in gray, considering that $E[d_k] = \frac{1}{\lambda_h}$, and $\frac{1}{\lambda_h} = 5T$, that is $\alpha = 5$.

Between two consecutive estimation time instants, there can be no observation data, illustrated by the red letter A, there can be one measurement, red letter B, or multiple measurements, shown in the red letter C. One example of such application is in target tracking, where inertial sensors that measure process input data such as linear acceleration and angular velocity operate at higher and regular frequencies compared to a network of GPS sensors, that are responsible for the observation model data.

On the next subsections, we discuss how the algorithm is executed for the scenarios when reliable time-stamp information is available, and when it is not present in the information package.

4.3.1 With Timestamp

If the estimator knows the exact time t_k that measurements were taken in a global timescale, *data assimilation* steps can be performed at the correct time instants. For that, the process model discretization given by (4.9) is performed considering variable time intervals δt_j^* , yielding

$$x(t_j^*) = f_d(x(t_{j-1}^*), u(t_{j-1}^*), w(t_{j-1}^*), t_{j-1}^*), \quad (4.93)$$

where t_j^* , $\forall j \in \mathbb{N}$ represents the estimation time sequence and is given by $t_j^* = t_{j-1}^* + \delta t_j^*$, with $t_0^* = 0$. The variable time interval δt_j^* is calculated according the schematic presented by Figure 4.3.

Each value δt_j^* corresponds to the time interval between the last instant t_{j-1}^* in which a signal was received, whether it transmitted input or observation data, and the next time interval t_j^* in which a new signal arrives. A zero order holder (ZOH) is used for input signals, considering last available information.

For the simulation carried out in Section 5, time intervals δt_j^* are calculated by uniting all arrival times for input and observation in a single vector, in an orderly fashion. The subtraction of consecutive time instants yields the time intervals sequence δt_j^* , $\forall j \geq 1$.

Since there are two signal types, input and observation, there are four possible cases for the estimator: input followed by another input; input followed by an observation; observation followed by an input; and observation followed by another observation. In Figure 4.2, all of them are represented. During the interval A , there are only input signals, so time interval is T and only *forecast* is performed. In the interval represented by B , we have to first execute complete *forecast* and *data assimilation* steps between input and observation, from $3T$ until t_1 , using $\delta t_4^* = t_1 - 3T$. Next, between an observation and an input signal, a ZOH is used for a *forecast* step between t_1 and $4T$. In other words, it is considered that the input remained constant between $3T$ and $4T$. When more than one observation arrive between two input signals, as in C , full *forecast* and *data assimilation* are performed as many times needed before one last *forecast* between the last observation and the next input signal.

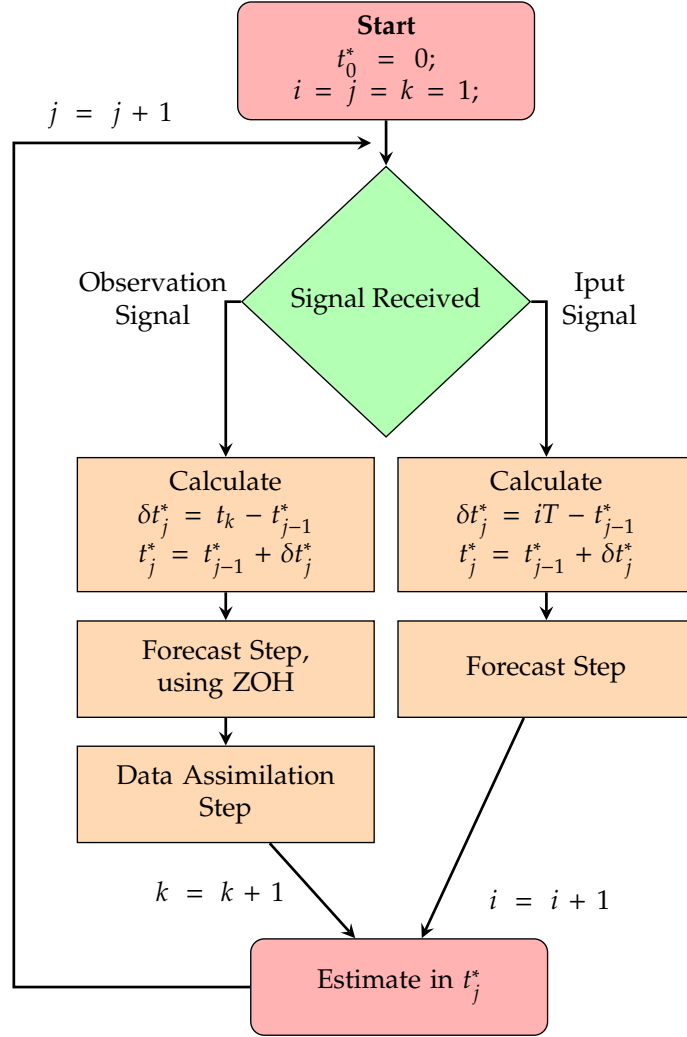


Figure 4.3: Illustrative schematic of the *online* estimator, with time-stamp. Indexes i , j and k represent the input, estimation and observation signal counters, respectively.

For the *online* estimator, the differential equations are numerically integrated as input or measurement signals arrive. In these instants, the corresponding time interval δt_j^* is calculated. If the current signal transmits input data, only the *forecast* step is executed. If it is observation data being received, both *forecast* and *data assimilation* steps are performed, considering a ZOH for the input data.

4.3.2 Without Timestamp

On the other hand, in case there is no information about time-stamp, process model (1.1) is discretized according to

$$x_n = f_d^*(x_{n-1}, u_{n-1}, w_{n-1}, n), \quad (4.94)$$

where $f_d^*(\cdot)$ represents the time-invariant discrete-time mode and $n = nT, \forall n \in \mathbb{N}$.

Since the estimator is not aware of the measurement time instant, *data assimilation* is always performed as the next input signal arrives, in a time instant multiple of T . In such cases, there are only two possible scenarios. One, in which there are no information between two consecutive input signal arrivals, represented by the letter *A* in Figure 4.2, when only *forecast* step is performed. If there is observation, full *forecast* and *data assimilation* steps are performed, considering the time interval T . In case illustrated by the letter *B*, measurement taken at time t_1 will be assimilated in time instant $4T$. When there are multiple measurements between two input signals, the oldest ones are discarded, as in letter *C*, for which the measurement taken at t_2 is discarded and the one taken at t_3 is assimilated at the instant $9T$.

4.4 Performance Metrics

In order to assess the performance degradation introduced by assimilating data at incorrect time instants, we need to define certain performance metrics for comparison. The algorithms described in Sections 4.2.2 and 4.2.1 estimate both the current state, $\hat{x}_{k|k}$ and its covariance matrix $\hat{P}_{k|k}^{xx}$. For the linear case, the *posterior* conditional PDF $\rho(x_k | (y_1, \dots, y_k))$ is Gaussian, according to (4.60), so it is fully characterized by its two first moments. Thus, if the filter is consistent, the following conditions shall be met (Bar-Shalom et al., 2001)

$$E[x_k - \hat{x}_{k|k}] \triangleq E[\tilde{x}_{k|k}] = 0, \quad (4.95)$$

$$E[(x_k - \hat{x}_{k|k})(x_k - \hat{x}_{k|k})^T] \triangleq E[\tilde{x}_{k|k}\tilde{x}_{k|k}^T] = P_{k|k}^{xx}, \quad (4.96)$$

where $\tilde{x}_{k|k}$ is the estimation error at time instant k . Condition (4.95) is called *unbiasedness* requirement, whereas (4.96) refers to *covariance matching*. For the non-linear case, these conditions cannot be fully met, since the *posterior* PDF is an approximation of a Gaussian density. Thus, the closer they are met, the more consistent are the filter results.

In this study we will use metrics that measure both consistency conditions. Ac-

cording to Bar-Shalom, in order to test them, the consistency criteria metrics for state estimation must certify: that state estimate errors are zero mean and compatible with the estimated state covariance; that innovations are also zero mean and compatible with their respective covariances; and that innovations are white. We will adopt two tests proposed by him that attests all conditions simultaneously, that is the normalized (state) estimation error squared (NEES) and normalized innovation squared (NIS) tests. We first defined NEES and NIS as

$$NEES_k \triangleq \tilde{x}_{k|k}^T (P_{k|k}^{xx})^{-1} \tilde{x}_{k|k}, \quad (4.97)$$

$$NIS_k \triangleq \eta_{k|k-1}^T (P_{k|k-1}^{yy})^{-1} \eta_{k|k-1}. \quad (4.98)$$

Under the linear and Gaussian assumption, we formulate a hypothesis test, under which the null hypothesis H_0 , that the filter is consistent, requires that both NEES and NIS follow chi-squared distributions, with n_x and n_y degrees of freedom, respectively, and n_x is the dimension of the state vector, whereas n_y is the dimension of the observation vector. The expected value of a RV that is chi-squared distributed is equal to its degrees of freedom quantity, that is $E[NEES_k] = n_x, \forall k > 1$ and $E[NIS_k] = n_y, \forall k > 1$.

We adopt single-run tests, thus for every estimation, we test the acceptance of H_0 , that is if both NEES and NIS at time instants k are within a certain interval, considering the accepted region as

$$P \{NEES_k \in [r_1, r_2] | H_0\} = 1 - \alpha, \quad (4.99)$$

$$P \{NIS_k \in [r_1, r_2] | H_0\} = 1 - \alpha, \quad (4.100)$$

where α is the significance level and interval $[r_1, r_2]$ is given by the chi-square distribution degrees of freedom and α . For instance, considering a system with a state vector of size 4 and observation vector of size 2, and a significance level of $\alpha = 5\%$, the acceptance intervals for NEES and NIS are respectively given by

$$[\chi_2^2(0.025), \chi_2^2(0.975)] = [0.051, 7.38], \quad (4.101)$$

$$[\chi_4^2(0.025), \chi_4^2(0.975)] = [0.484, 11.1], \quad (4.102)$$

which means that, if the filter is consistent, in 95% of the estimates, NEES and NIS value should fall under their correspondent intervals. Figure 4.4 shows both χ^2_2 and χ^2_4 PDFs, with the 95% acceptance region.

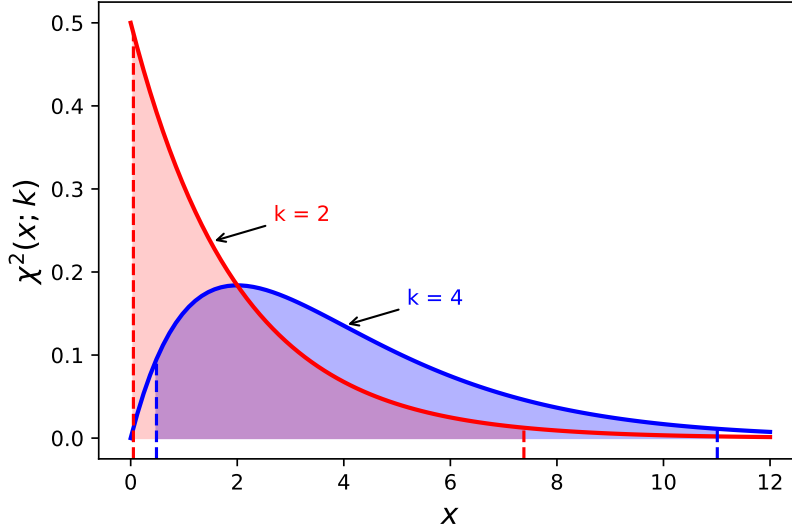


Figure 4.4: χ^2 PDFs for 2 (red) and 4 (blue) degrees of freedom. The vertical dashed lines represent the acceptance interval limits, for $\alpha = 5\%$, and the shaded area is the corresponding acceptance regions.

Additionally, since we are using simulated systems, the root mean square error (RMSE) of the system states will also be calculated as an accuracy performance index, given by

$$RMSE = \frac{\sum_{i=1}^N \sqrt{(\hat{x}_{k|k} - x_k)^2}}{N} \quad (4.103)$$

where x_k is the true state vector and N is the amount of estimates.

4.5 Simulation Scenarios Design

To evaluate performance and consistency effects of the aperiodic sampling in state estimation, we study three scenarios: variation of measurement SNR; variation of λ ; and variation of T . First scenario intends to study how the effects vary for higher noise levels in the observation model. The second scenario assess how the average sampling rate of measurements affect the degradation in performance when time-stamp is and

is not considered in state estimation. In the last simulation scenario we study the behavior of the effects when the regular estimation time interval distances itself from the average sampling rate of the observations.

Since estimation is performed in the presence of random quantities, simulations need to be performed throughout several runs, so that confidence intervals can be constructed towards more consistent conclusions. Average values for accuracy J and consistency $NEES$ and NIS performance indexes are calculated with corresponding 95% confidence intervals.

Numerical Results

In this chapter, we present state estimation simulation results for two different sampled-data systems: a linear system with two under damped modes and a non-holonomic unicycle position system. We begin by describing them as state-space representations. Then, we discuss their characteristics and present realization examples to illustrate simulation runs.

For both cases, we start evaluating the effect of time-stamp information in the estimation algorithm for three different irregular sampling scenarios: variation of the observation signal-to-noise ratio, variation of the observation average sampling rate, and variation of the relation between estimation regular sampling rate and output irregular average sampling rate. Performance metrics defined in Section 4.4 are used for comparison.

Since simulations are carried out in digital computers, it is impossible to simulate the continuous-time variables of the sampled-data systems. Therefore, we try to reproduce true values of the states by choosing very small time steps δt_{sim} to simulate the real data, especially since the system is observed with continuous-time randomly spaced intervals.

5.1 Linear System

Our first choice of system is a fourth-order LTI system, since its results are predictable and difference equations calculations have an exact solution, thus comparison and results assessment are expected to be more clear and comprehensive. Additionally, we choose the combination of two independent modes, each of second order and with distinct dynamics, so the effects can be evaluated separately.

5.1.1 System Description

The linear system designed for simulation is the serial combination of two second order under damped modes, with different band pass behaviors.

One of the modes, henceforth termed as low-pass (lp) system, has time constant $\tau_{lp} = 1$ s, natural frequency $\omega_{n,lp} = 10$ Hz and a damping constant of $\zeta_{lp} = 0.1$. The frequency response is given by:

$$G_{lp}(s) = \frac{100}{s^2 + 2s + 100} \quad (5.1)$$

The second mode is a high-pass (hp) system, with a much lower time constant $\tau_{hp} = 0.01$ s, natural frequency $\omega_{n,hp} = 1000$ Hz, same damping constant of $\zeta_{hp} = 0.1$ and two zeros, one at the origin and another one at 0.001. The high-pass frequency response is given by:

$$G_{hp}(s) = \frac{s^2 - 0.001s}{s^2 + 200s + 10^6} \quad (5.2)$$

Figure 5.1 shows the bode diagrams of both systems separately.

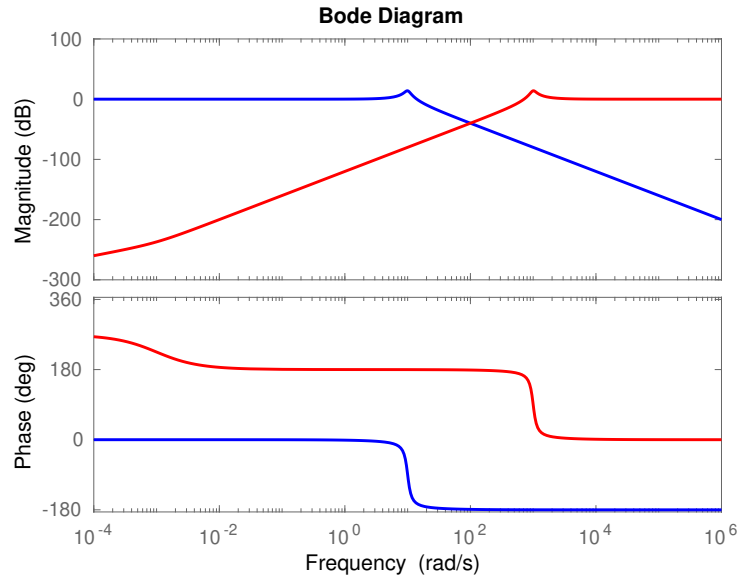


Figure 5.1: Bode diagram of both modes. Blue represent the low-pass system and red the high-pass system.

The resulting fourth order system is described as a state space representation, in a modal canonical form given by:

$$\dot{x}(t) = Ax(t) + Bu(t) \quad (5.3)$$

$$y(t) = Cx(t) + Du(t) \quad (5.4)$$

where $x(t) \in \mathbf{R}^4$ is the state vector, $u(t) \in \mathbf{R}^1$ is the single input vector and $y(t) \in \mathbf{R}^1$ is the single output vector, and

$$A = \begin{bmatrix} -100 & 994.99 & 0 & 0 \\ -994.99 & -100 & 0 & 0 \\ 0 & 0 & -1 & 9.949 \\ 0 & 0 & -9.949 & -1 \end{bmatrix}, \quad (5.5)$$

$$B = \begin{bmatrix} -24.6435 \\ -18.8943 \\ -4.1746 \\ -0.2675 \end{bmatrix}, \quad (5.6)$$

$$C = [24.41 \quad -21.2522 \quad -0.1537 \quad 2.3977], \quad (5.7)$$

$$D = 1. \quad (5.8)$$

We simulate a pseudo-random binary sequence (PRBS) as input, with 200 samples, as shown in Figure 5.2.

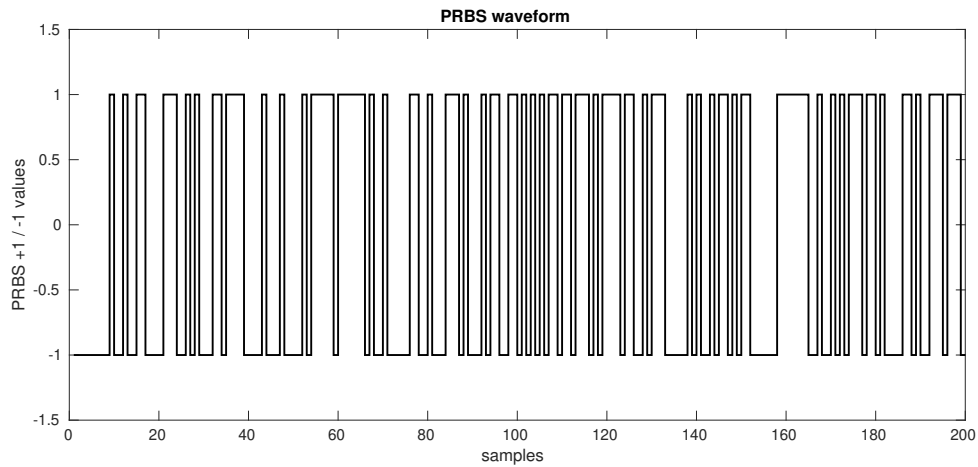


Figure 5.2: 200 PRBS samples used as input

The PRBS signal is used as input to the low-pass and high-pass systems separately, considering two different time frames, of 2 and 20 seconds. The results of the four linear simulations are shown in Figure 5.3. We can see a much faster response from the high-pass filter in both cases, as expected.

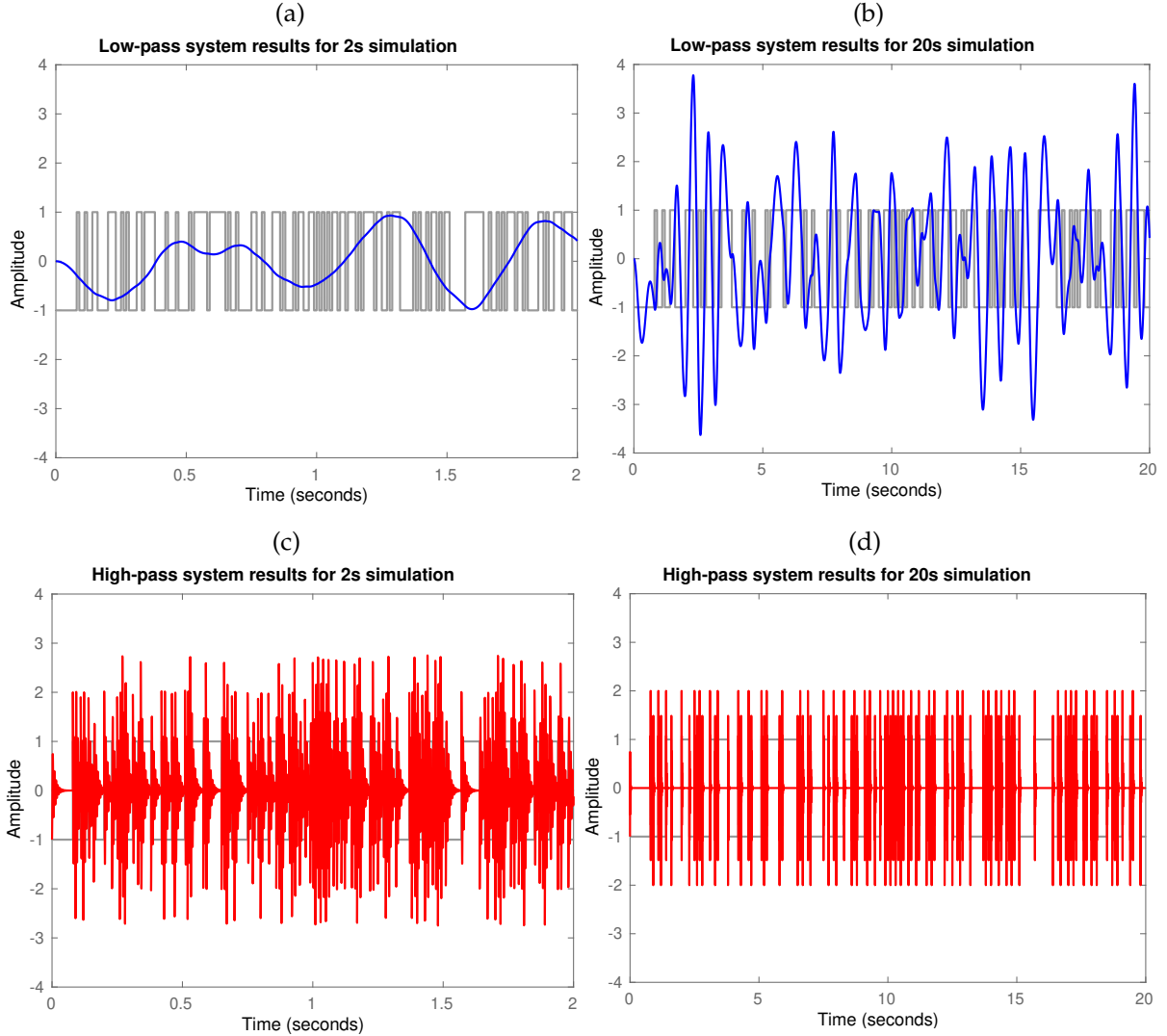


Figure 5.3: Linear simulation results of the low-pass and high-pass systems separately. Grey lines represent the PRBS input and colored lines the output. Graphs (a) and (b) with blue outputs represent the results of the low-pass system; and (c) and (d) with red outputs, the results of the high-pass system. Graphs on the left show a time frame of 2 seconds of simulations, whereas the ones on the right are the result of a 20 seconds time frame; considering the same 200 samples of PRBS for all four simulations.

The 20 seconds simulation for the high-pass system generates outputs that stabilize very quickly, with a dynamics hard to be observed. Thus, we choose the 2 seconds time

frame to simulate the fourth order serialized systems, given by (5.3)-(5.8). The result of the linear simulation of the fourth order system is presented in Figure 5.4.

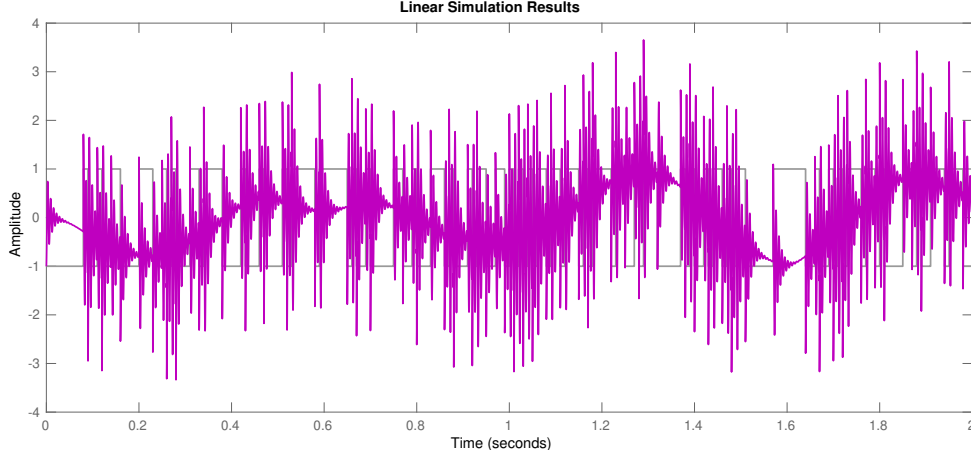


Figure 5.4: Output of the fourth order system to the PRBS input signal over a 2 seconds time frame.

System discretization is performed using MatlabTM's built-in function `c2d` to produce a discrete-time state space representations according to

$$x(t_{k+1}) = A_d(t_k)x(t_k) + B_d u(t_k) + w(t_k), \quad (5.9)$$

$$y(t_k) = B_d x(t_k) + D_d u(t_k) + v(t_k) \quad (5.10)$$

where $\rho(v(t_k)) = \mathcal{N}(0, R)$ and $\rho(w(t_k)) = \mathcal{N}(0, Q)$ are, respectively, the process and observation noise, with zero mean and covariance R and Q . When time-stamp is not available, the observation vector is approximated by $\tilde{y}_i \approx y(t_k)$, where i is the index of the next time instant, multiple of T . When it is available, discretization is performed using variable time intervals.

5.1.2 Linear System Realization

In this section we present one realization of the state estimation simulation for the system defined by (5.3)-(5.8), the Kalman Filter described in Section 4.2.1 and the algorithms modifications explained in Section 4.3.

The parameters are set according to

$$\delta t_{\text{sim}} = 10^{-6} \text{ s}, \quad (5.11)$$

$$T = 2 \times 10^{-3} \text{ s}, \quad (5.12)$$

$$\lambda = 500 \text{ Hz}, \quad (5.13)$$

$$SNR_{\text{obs}} = 30 \text{ dB}, \quad (5.14)$$

$$SNR_{\text{pro}} = 30 \text{ dB}, \quad (5.15)$$

where δt_{sim} is the real system data simulation time-step, T is the regular estimation and input sampling time interval, λ is the parameter of Poisson process that describes time instants sequence t_k , $\forall k \in \mathbb{N}$ and SNR_{obs} and SNR_{pro} are the signal-to-noise ratio of the observation and process models, respectively. Noise is generated using the `awgn` function from Matlab™. For this realization, it resulted in a measurement noise variance of $R = 9.596 \times 10^{-4}$ and process noise variance of $Q = 9.986 \times 10^{-4}$. These exact values were used in the Kalman filter implementation and the estimation results for states x_1 and x_4 of the algorithms with and without timestamp, in comparison to the true state values are shown in Figures 5.5.

For the high-pass system state x_1 , it is hard to note a significant difference in the estimation performance. However, for state x_4 , from the low-pass system, the degradation is visible for the algorithm that does not acknowledge time instants t_k information in the estimation process.

Figure 5.6 presents a window data from 0 to 0.013 seconds of state x_2 RMSE for the algorithms with and without time-stamp. As expected, we observe a distancing from the RMSE at the instant the first observation was taken t_1 , favoring the algorithm that considers time-stamp. For the time period without observations, the algorithms' RMSE evolve in a similar way. When measurements start to appear back again, we can notice further degradation in the performance when time-stamps are not considered.

Finally, for this realization, we also present in Figure 5.7 the single-run consistency tests NEES and NIS as defined in Section 4.4. In each graph, the acceptance intervals is marked by horizontal lines. The upper plots (a) and (b) represent the NEES and NIS values, respectively, for the algorithm that considers time-stamp in the estimation process. We can see that the estimates are quite consistent, with the values inside the acceptance region most of the time. In fact, the null hypothesis rejection rate, that is the

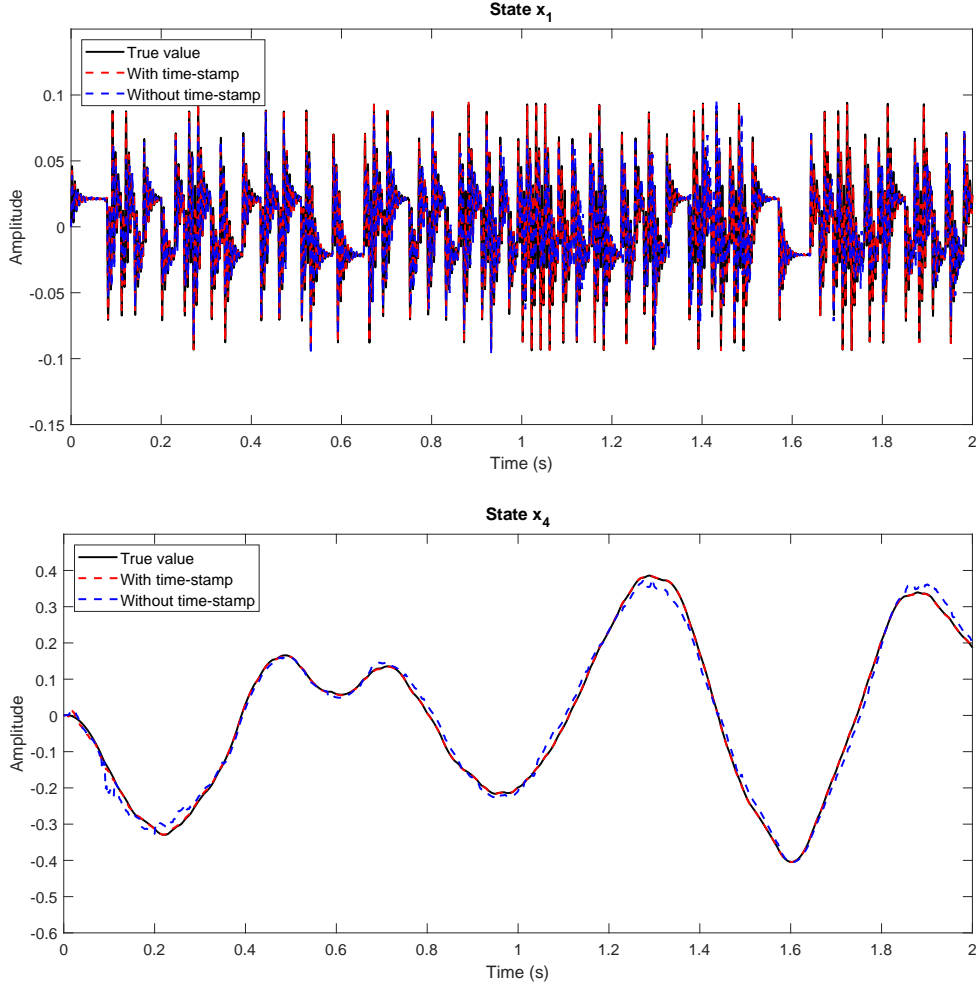


Figure 5.5: States x_1 and x_4 estimates with time-stamp (---), without time-stamp (---) and true values (—).

proportion of times the values were out of their acceptance region, was 0.04 for NEES, and 0.055 for NIS, very close to the 0.05 expected. When time-stamp information was not available, consistency was heavily degraded, with rejection rates escalated to 0.61 and 0.43, respectively. Moreover, NEES and NIS values were so high in some occasions, that the acceptance region is hardly visible in the graphs. In practice, such a consistency degradation means that estimation covariances are highly underestimated.

In the next sections we study the scenarios described in Section 4.5. Only one state per mode is evaluated, namely x_1 and x_4 , for simplicity.

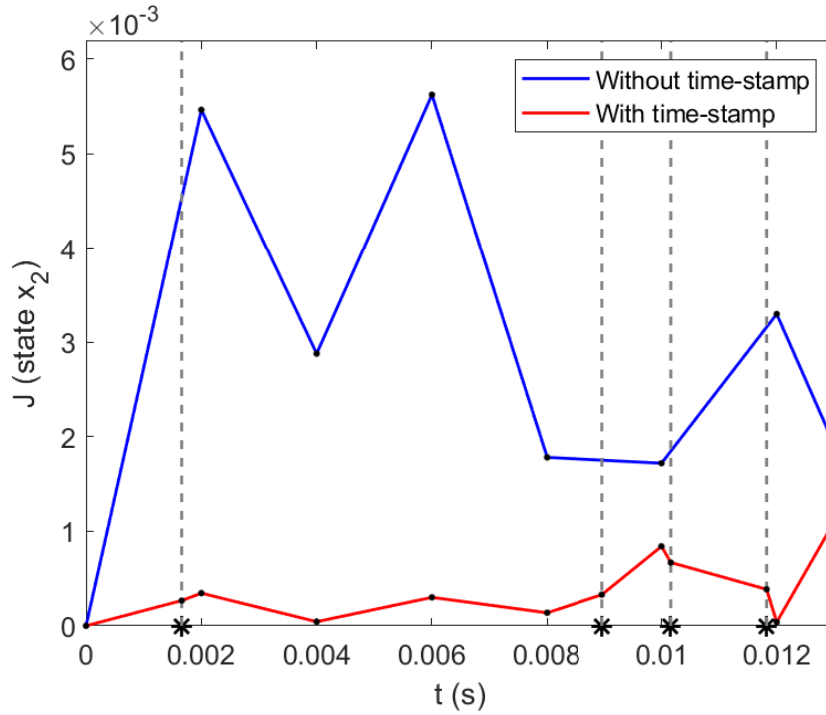


Figure 5.6: Temporal cut from 0 to 0.013 seconds, for a realization of state x_2 RMSE of both estimators, with (—) and without (—) time-stamp. Vertical dashed lines match the measurement sampling instants t_k . Black dots represent the estimation instants.

5.1.3 Measurement Signal-to-Noise Ratio Variation

For the first simulation scenario, we consider SNR variation of 60, 50, 40, 20, and 10, dB both for the process and observation models. Regular estimation time interval T is maintained fixed at $T = 0.002$ s and $\alpha = 1$, thus $\lambda = 500$ Hz. For a 100-run simulation, obtained results for accuracy and consistency are presented in Figure 5.8 with the corresponding 95% confidence intervals.

Results suggest that for higher SNR levels, that is less noise present in data, taking into account time-stamp information plays an important role, both for accuracy and consistency. When noise levels increase, indexes approximate for both algorithms. Consistency tests for the algorithm with time-stamp remains almost constant for all SNR values, whereas for the algorithm without time-stamp they decrease to values that do not differ statistically from both methods.

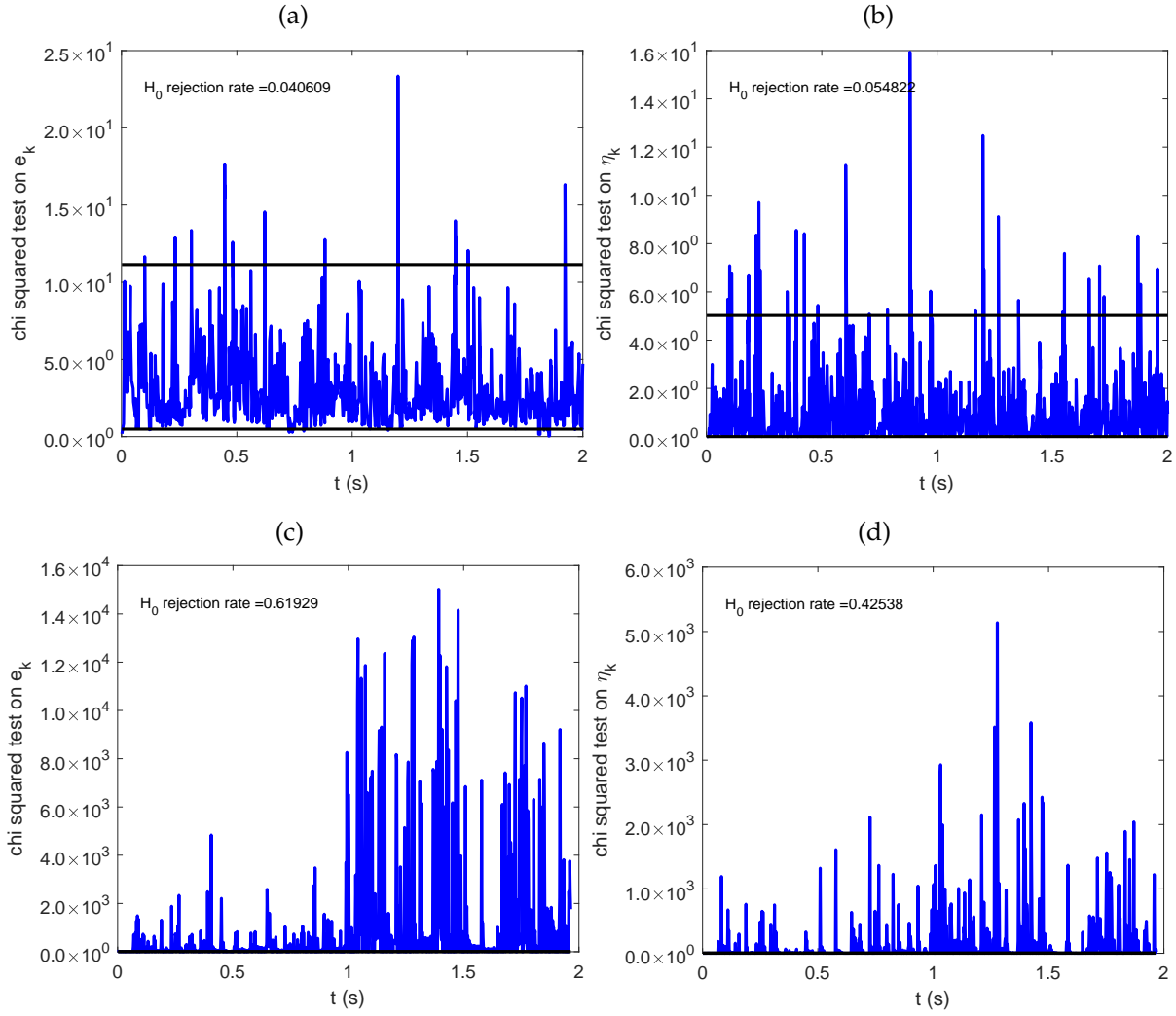


Figure 5.7: Consistency tests NEEs and NIS for the linear system state estimation with time-stamps (a) and (b); and without time-stamp (c) and (d). Horizontal lines define the acceptance region upper and lower limits, for a significance level $\alpha = 0.05$. In each graph, the null hypothesis H_0 rejection rate is also presented.

5.1.4 Average Sampling Rate Variation

In the second simulation scenario for the linear system, we consider an average sampling rates of observation variation of $\lambda = 0.001, 0.002, 0.05$, and 0.1 Hz. Relation between λ and T is kept constant $\alpha = 1$. SNR levels for process and observation models are chosen to be $SNR_{\text{obs}} = SNR_{\text{pro}} = 30$ dB. Simulation was carried out 100 times and performance indexes for accuracy and consistency are shown in Figure 5.9 with corresponding 95% confidence intervals.

In this case, the smaller the λ the higher is the difference in algorithm performances,

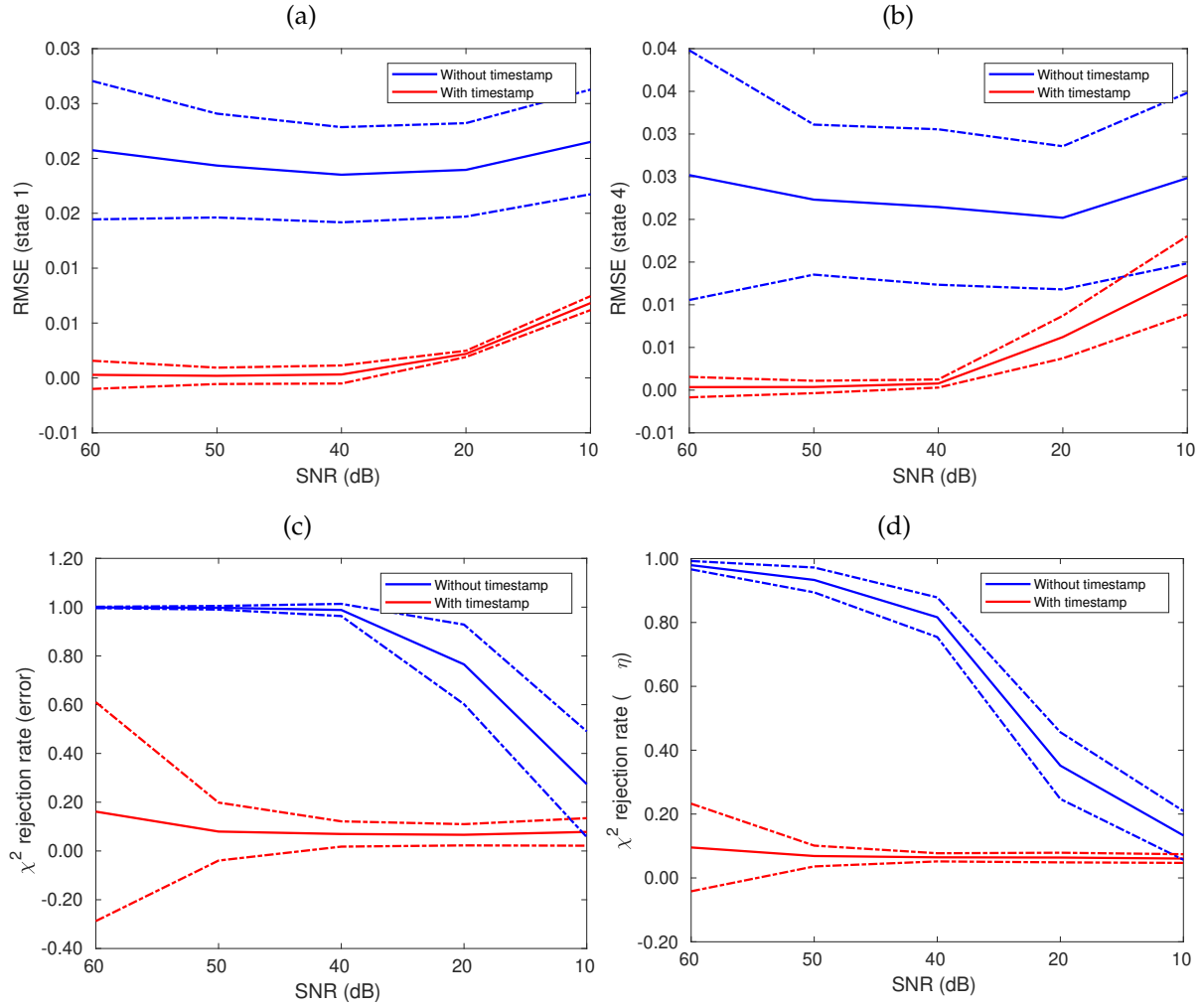


Figure 5.8: Linear system estimation performance indexes with 95% confidence intervals, as a function of input and observation SNR, for algorithms with (—) and without (---) time-stamp. Accuracy values for states x_1 and x_2 are shown in (a) and (b), respectively. Consistency results are in (c) and (d) for NEES and NIS tests, respectively.

in favor of the one that considers time-stamp information. The high values used for simulation caused both algorithms to perform with no statistically significant difference. It suggests that, the more spaced time intervals of observations, the bigger is the importance of incorporating time instant information in the estimation process. That can be explained by the fact that in such cases, the approximation error of t_k is higher and so is the additional noise introduced by data assimilation performed at incorrect time instants.

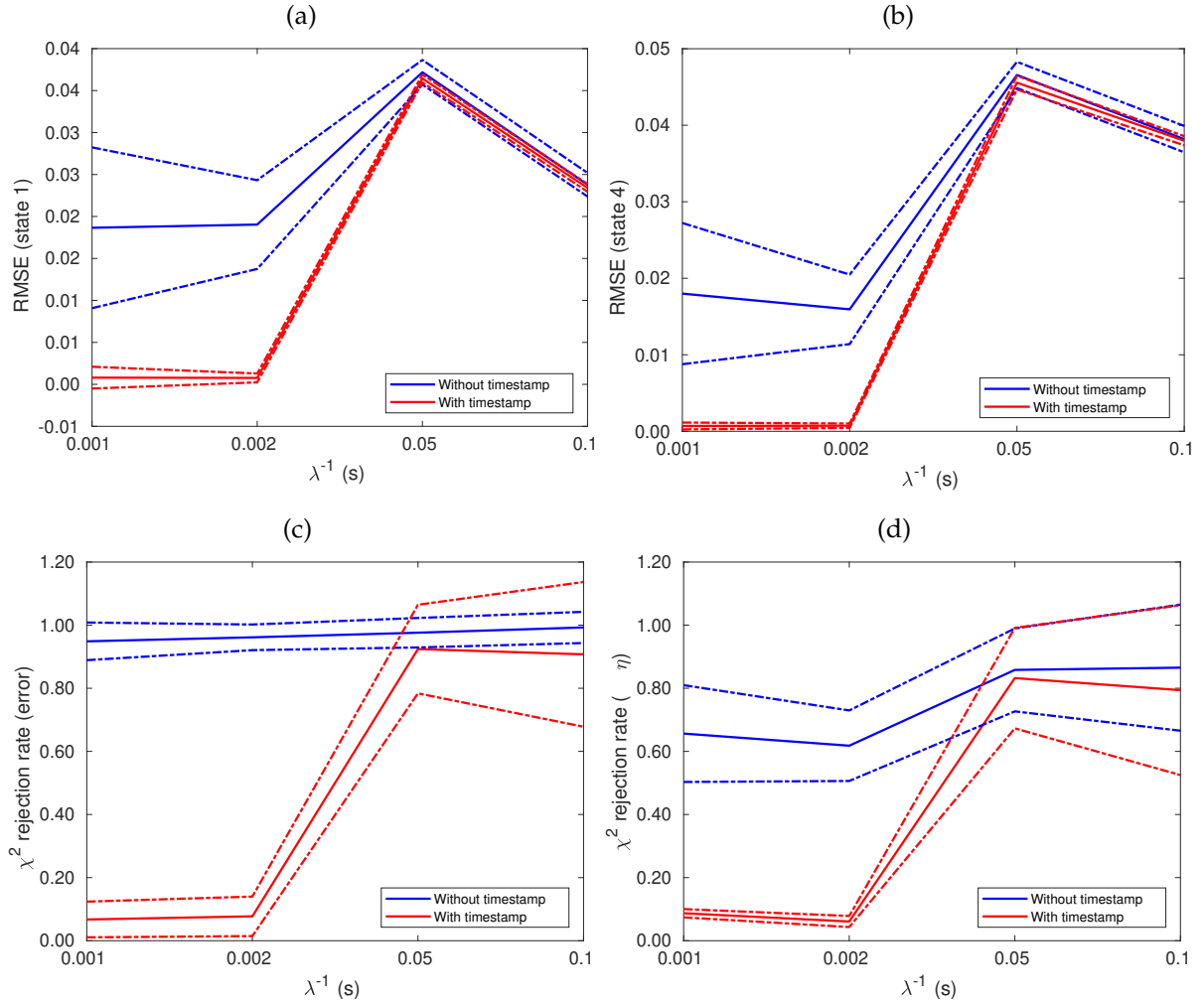


Figure 5.9: Linear system estimation performance indexes with 95% confidence intervals, as a function of average time interval λ^{-1} , for algorithms with (—) and without (---) time-stamp. Accuracy values for states x_1 and x_2 are shown in (a) and (b), respectively. Consistency results are in (c) and (d) for NEES and NIS tests, respectively.

5.1.5 Regular and Average Irregular Time Interval Relation Variation

The last linear system case study is simulated considering a variation of $\alpha = 5, 3, 2$, and 1 . Other parameters are kept constant, namely $\lambda = 500$ Hz, and $SNR_{\text{obs}} = SNR_{\text{pro}} = 30$ dB. Once again, a 100-run simulation is performed and results are shown in Figure 5.10.

In this case, performance remained almost constant both for accuracy and consistency, when time-stamp information was available, suggesting that it does not depend on α values. On the other hand, results for the algorithm that does not consider time-stamp are better when regular estimation sampling rate is higher. That is, when input

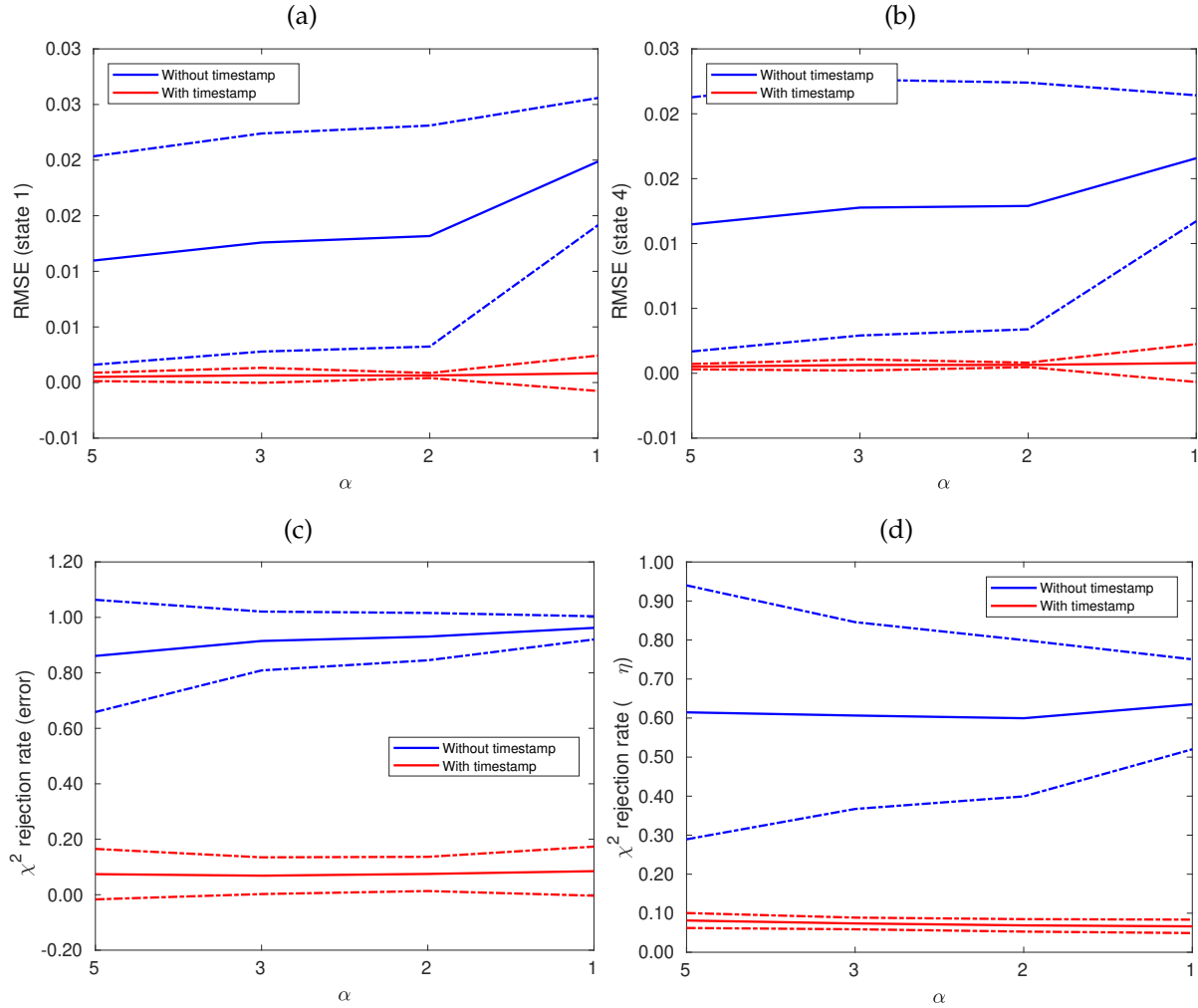


Figure 5.10: Linear system estimation performance indexes with 95% confidence intervals, as a function of α , for algorithms with (—) and without (---) time-stamp. Accuracy values for states x_1 and x_2 are shown in (a) and (b), respectively. Consistency results are in (c) and (d) for NEES and NIS tests, respectively.

information is available at faster rates than the average sampling rate of observations, knowing the exact time instant t_k becomes less important.

5.2 Unicycle Position Estimation

Falta incluir os resultados dos testes NEES e NIS

We now consider a non-linear system given by a nonholonomic moving robot, which position in the xy -plane we want to estimate. In many real target tracking problems such as this, measurements are available by unsynchronized cameras through an

internet network, for instance. Or multiple GPS sensors might be used in a centralized architecture without data alignment and association. These configurations are keen to sampling irregularities, which motivates our choice.

5.2.1 System Description

Consider a nonholonomic moving robot, with the cinematic process model given by

$$\begin{aligned}\dot{p}_x &= v \cos(\theta), \\ \dot{p}_y &= v \sin(\theta), \\ \dot{\theta} &= u_1(t), \\ \dot{v} &= u_2(t),\end{aligned}\tag{5.16}$$

where p_x and p_y are the position coordinates, θ the angular orientation, v the linear velocity and inputs u_1 and u_2 are the angular velocity ω and the linear acceleration a , respectively. Figure 5.11 shows a schematic of the robot and its states,

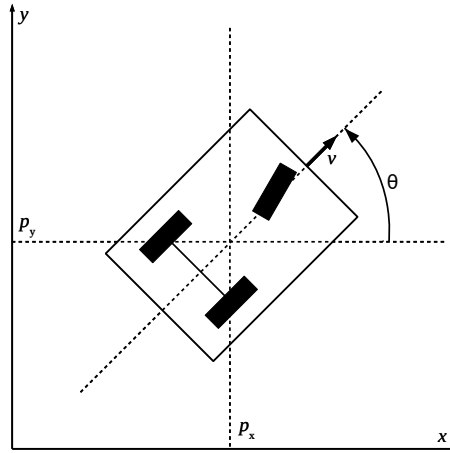


Figure 5.11: Nonholonomic robot system representation. The system states p_x , p_y , v and θ are highlighted.

The system described by 5.16 is discretized by a fourth order Runge-Kutta method as described in Section 4.1 and the state vector x_i is given by $x_i \triangleq [p_{x,i} \ p_{y,i} \ \theta_i \ v_i]^T$.

The observation model $y(t_k) \in \mathbb{R}^2$

$$y(t_k) = \begin{bmatrix} p_x(t_k) \\ p_y(t_k) \end{bmatrix} + v(t_k), \quad (5.17)$$

is given by the position coordinates and $\rho(v(t_k)) = \mathcal{N}(0, R_{t_k})$ is the observation noise, with zero mean and covariance R_{t_k} . When time-stamp is not available, the observation vector is approximated by $\tilde{y}_i \approx y(t_k)$, where i is the index of the next time instant, multiple of T .

Input vector $u_i = [\omega_i \ a_i]^T$ is measured by a girometer and accelerometer, respectively. We assume that

$$u_i = \tilde{u}_i - w_i, \quad (5.18)$$

where \tilde{u} represent the sensors' measured values and $\rho(w) = \mathcal{N}(0, Q_i)$ is the corresponded noise, of zero mean and covariance Q_i .

We simulate 60 seconds of robot movement, considering a step size of $\delta t_{\text{sim}} = 10^{-4}$. Irregular sampling time intervals h_k are simulated by the exponential probability distribution function from Matlab™ and approximated to the nearest discrete time instant, from the 600,000 available samples. Input signals were generated arbitrarily according to Figure 5.12. Figure 5.13 shows robot trajectory on xy -plane for the given input signals, leaving from point $(0,0)$, as well as a realization of noisy and aperiodic measurements with signal-to-noise ratio of $\text{SNR}_y = 30$ dB and $\lambda = 3.33$ Hz as red dots and the hatched blue line represents UKF estimation, considering time-stamp, $\alpha = 5$ and $\text{SNR}_u = 10$ dB.

To analyze the effect of assimilating data at incorrect time instants in the estimation algorithm, we use the performance index J

$$J = \frac{\sum_{i=1}^N \sqrt{(\hat{p}_{x,i} - p_{x,i})^2 + (\hat{p}_{y,i} - p_{y,i})^2}}{N} \quad (5.19)$$

where $\hat{p}_{x,i}$ and $\hat{p}_{y,i}$ are filter position estimates produced at a regular interval T , $\hat{p}_{x,i}$ and $\hat{p}_{y,i}$ the true coordinates of the robot at the same time instants and N the total number of estimates. This index represents the average estimator position error in xy -plane, similar to RMSE.

Figure 5.14 shows a timespan from 0 to 1.3 seconds of a J realization, considering $\lambda = 0.5$, $\alpha = 5$, $\text{SNR}_y = 60$ dB and $\text{SNR}_u = 20$ dB, for the UKF considering and not considering time-stamp. Black dots represent the regular time instants kT whereas the

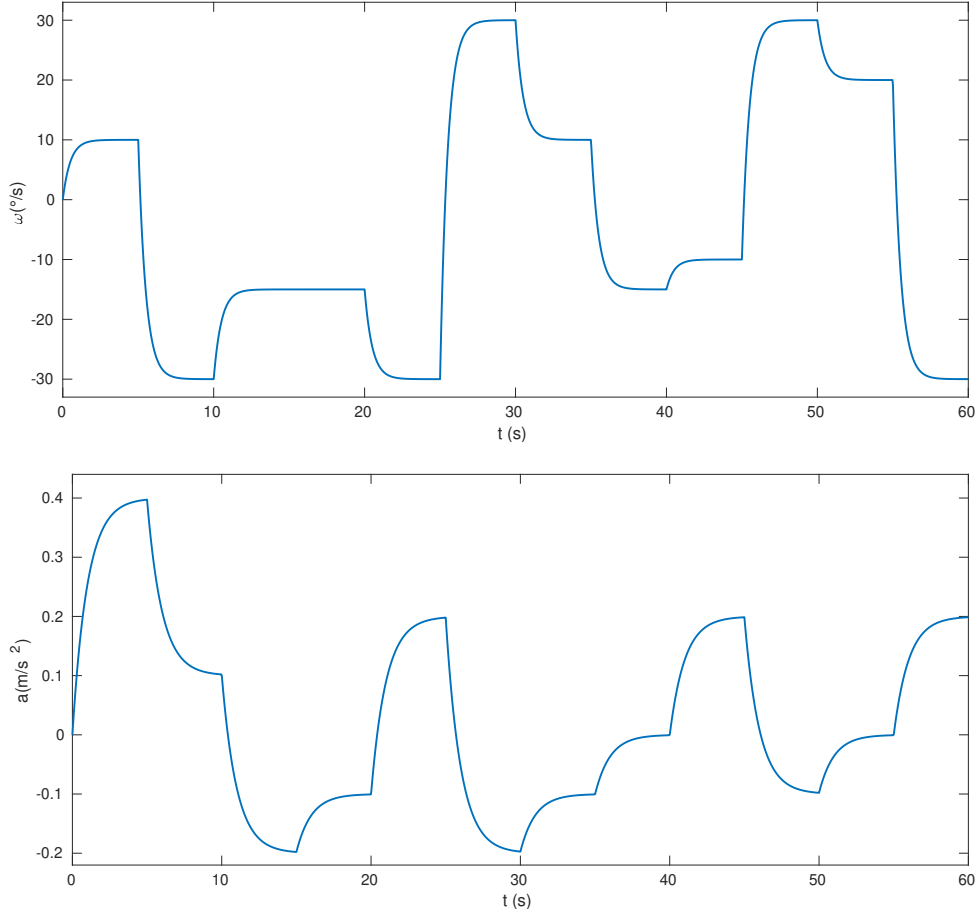


Figure 5.12: Simulation input signals. (a) shows temporal sequence of angular velocity ω and (b) shows linear acceleration a .

asterisks on x-axis match the exact measurement instants t_k . As expected, before the first data assimilation steps, both performances are identical. Since the first measurement t_1 was taken almost at the same time as regular estimation time instant $4T$, both estimation performances maintain close to each other. That is because the approximation error due to $\tilde{y}_i \approx y(t_k)$ is irrelevant. At t_2 we can observe significant deviation from index J in benefit of the algorithm considering time-stamp, since it performs data assimilation at the exact time measurement was taken. The same effect can be noted at t_4 , after 1 second of simulation, when there is a significant different between time the measurement was taken and the next regular estimation instant.

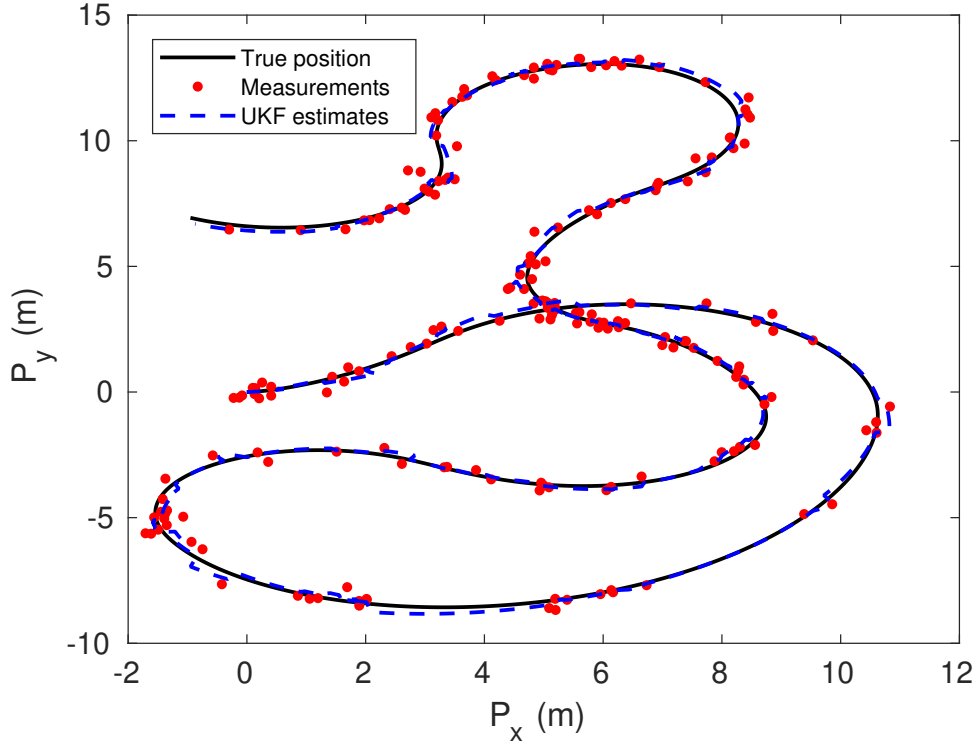


Figure 5.13: True position, noisy measurements and UKF estimates considering time-stamp, for a measurement noise of $\text{SNR}_y = 30$ dB, $\lambda = 0.3$ s and $\alpha = 5$.

5.2.2 Measurement Signal-to-Noise Ratio Variation

In this subsection we compare the estimation performance impact of considering time-stamp in the algorithm, by varying the measurement noise level. The signal-to-noise ratio for the input sensors and the measurement average time interval are held constant, $\text{SNR}_u = 20$ dB and $\lambda = 0.1$ s.

We considered an observation signal-to-noise variation of $\text{SNR}_y = \infty, 80, 60, 40, 20, 10$ dB. That is, initially the system was simulated considering no measurement noise and then it was gradually increased. For each noise scenario, we ran 100 realizations of the random variables for each algorithm and Figure 5.15 shows the results. Solid lines represent the average values for J and the dashed lines are the 95% confidence interval.

Only for small noise levels, that is high SNR values, there are statistically significant difference between performances, in favor of knowing the exact time-instants. When SNR_y is infinite or as high as 80 dB, the performance index J accuracy difference is approximately 1.25 and 1.26 cm, respectively. For SNR values lower than 40 dB, however, it is not possible to distinguish among performances of both estimators.

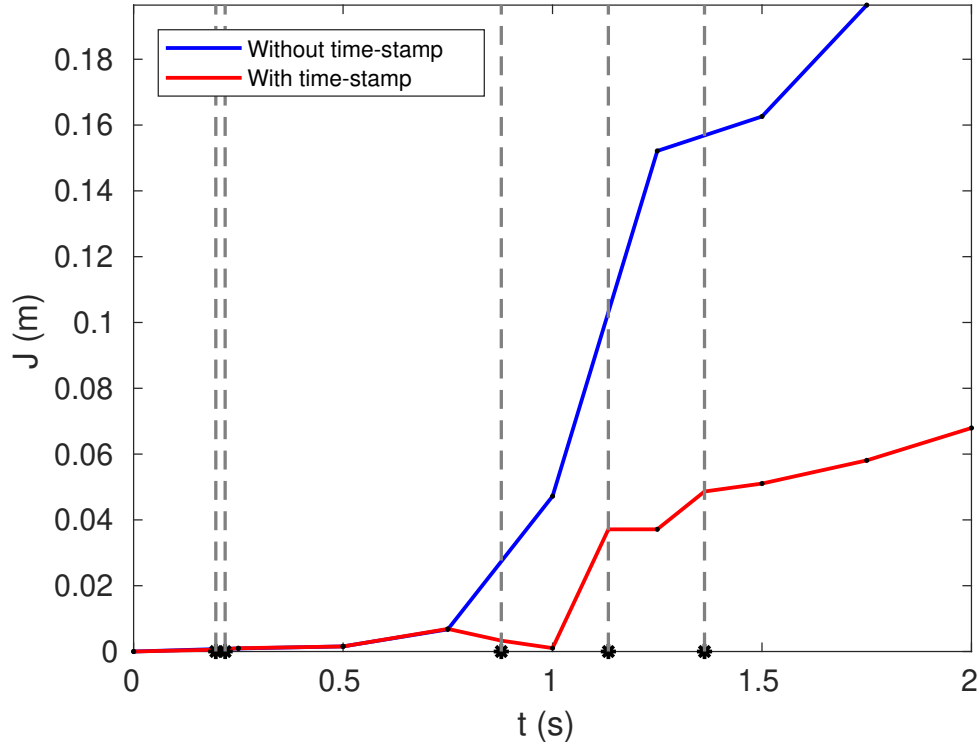


Figure 5.14: Temporal cut from 0 to 1.3 seconds, for a realization of J of both estimators, with and without time-stamp. Asterisks on x axis match the measurement sampling instants t_k . Black dots represent the regular estimation instants, same as input regular sampling instants.

5.2.3 Average Sampling Rate Variation

We now consider the variation of the average time interval that observations are taken, according to $\lambda = 0.1, 0.2, 0.3, 0.4, 0.5, 0.6$ s, maintaining the other parameters constant, namely the noise level of inputs and observations, $\text{SNR}_u = 20$ dB and $\text{SNR}_y = 40$ dB, respectively. We carried out 100 realizations for each λ and for each algorithm and Figure 5.16 presents the results. Again, the solid lines are the average values of J and the 95% confidence interval is between the dashed lines.

Results show that performance degradation is more significant for more spaced time intervals, if dynamics and other parameters are kept fixed. For higher $\frac{1}{\lambda}$ rates, there are no statistical differences in performance. As average time interval grows, degradation increases and it starts to be apparent, reaching mean differences of 3.1 cm for a $\lambda = 1.667$ Hz. One possible explanation derives from the fact if average sampling rate is considerably higher than system dynamics speed, time instant t_k approximations errors are reduced. In such cases, sensor noise might end up being much more relevant

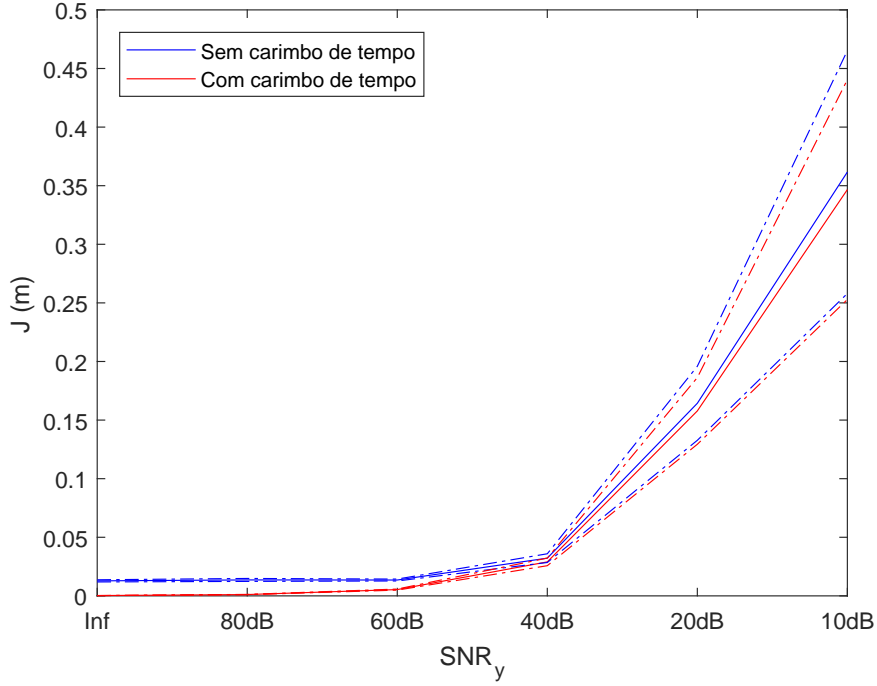


Figure 5.15: Performance index J variation, as a function of measurement noise for both UKF algorithms considering and not considering time-stamp

than the error tunned by assimilating data at incorrect instants.

5.2.4 Regular and Average Irregular Time Interval Relation Variation

We also analyze the performance impact of varying the parameter α , which is the relation between regular input time interval T and average measurements time interval λ . The simulated values were $\alpha = 10, 5, 2, 1$. That means we start with higher frequency values for input sampling in comparison to measurement sampling and this values is gradually decreased. Other parameters were maintained constant $\text{SNR}_u = 20$ dB and $\text{SNR}_y = 40$ dB.

The same way we did for the other scenarios, 100 realizations were simulated and Figure 5.17 presents the results. Solid lines are the average values for J and dashed lines represent the 95% confidence interval.

The same way as it happened for the linear system, results suggest that when exact time instants t_k are available, variations of α do not impact estimation performance. On the other hand, when time-stamp is not considering in the estimation process, the relation between regular estimation and average measurement time intervals plays

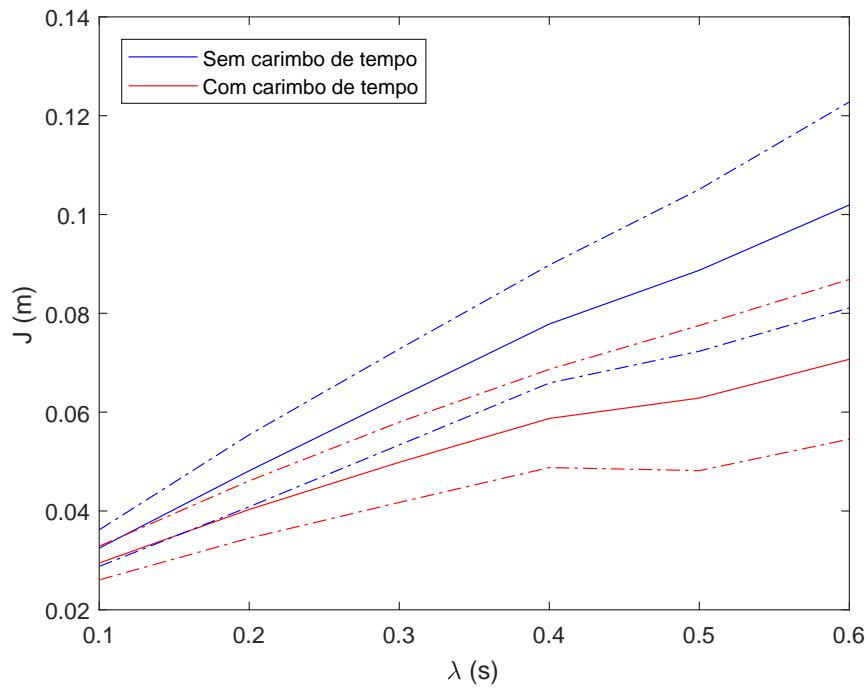


Figure 5.16: Performance index J variation, as a function of measurement noise both UKF algorithms considering and not considering time-stamp

an important role in estimates accuracy. The higher is the regular estimation rate in comparison to measurement rate, smaller is the degradation. In fact, for α values of 10 and 5, performances are statistically indistinguishable. When rates are the same, position estimate error doubled for the algorithm that does not consider time stamp. Such phenomenon can be explained by the fact that higher α values lead to smaller time steps used in the process model discretization in comparison to the measurement time intervals. Thus, approximation error originated from $\tilde{y}(i) \approx y(t_k)$ is reduced.

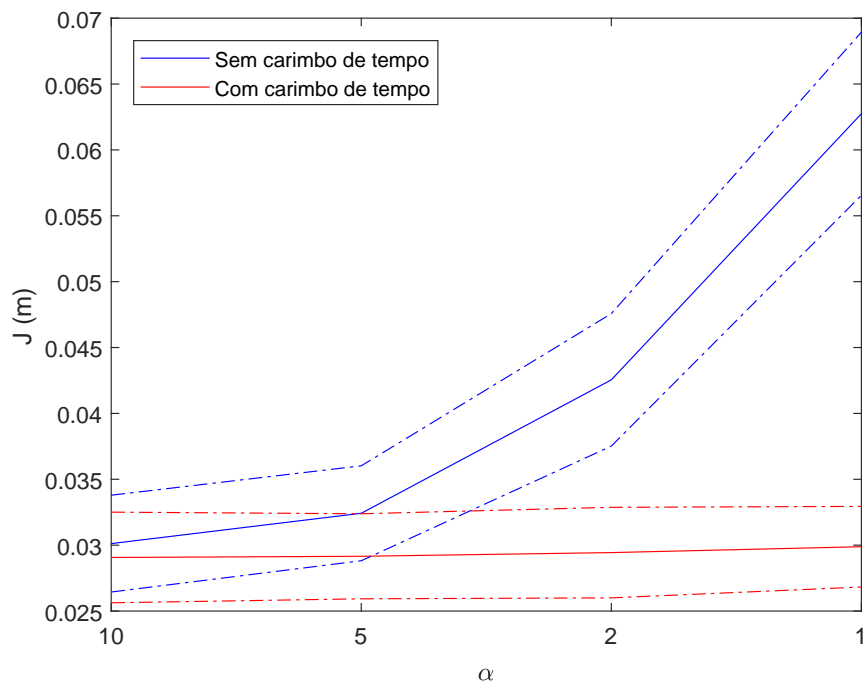


Figure 5.17: Performance index J variation, as a function of λ for both UKF algorithms considering and not considering time-stamp

Conclusions

Falta conclusão

6.1 Project Overview

Investigou-se isso e aquilo... (caso algum leitor pule direto para a conclusão)

6.2 Main Results

Como os resultados corroboram os objetivos perseguidos. O que é relevante dizer sobre cada objetivo descrito no capítulo 1, com o que foi feito no trabalho.

Autocrítica sobre o trabalho: alguma hipótese foi pouco realista? o que não foi feito tão bem? o que foi feito bem?

6.3 Future Work

Talvez uma lista itemizada Trabalhos futuros podem vir diretamente da autocrítica.

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