

## DESCRIPTION

The MP3422 is a high-efficiency, synchronous, current-mode, step-up converter with output disconnect.

The MP3422 starts up from an input voltage as low as 1.9V, while providing inrush current limiting and output short-circuit protection. The integrated P-channel synchronous rectifier improves efficiency and eliminates the need for an external Schottky diode. This P-channel disconnects the output from the input during shutdown.

The 600kHz switching frequency allows small external components, while the internal compensation and soft-start minimize external component count. The MP3422 provides a compact solution for a 5V output, 2.5A load requirement, using a supply voltage down to 2.8V.

The MP3422 is available in 14-pin QFN 2mmx2mm package.

## FEATURES

- Up to 98% Efficiency
- 1.9V to 5.5V Input Range
- 2.5V to 5.5V Output Range
- Internal Synchronous Rectifier
- 600kHz Fixed Switching Frequency
- >6.5A Switch Current Limit Capability
- 43uA Quiescent Current
- High Efficiency over Full Load Range
- Internal Soft-start and Compensation
- True Output Load Disconnect from Input
- OCP, SCP, OVP and OTP Protection
- Small 2x2mm QFN14 Package

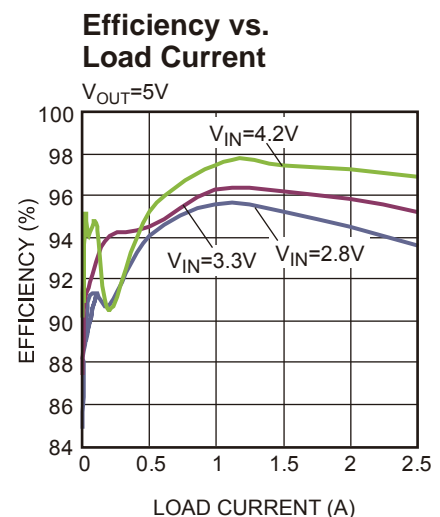
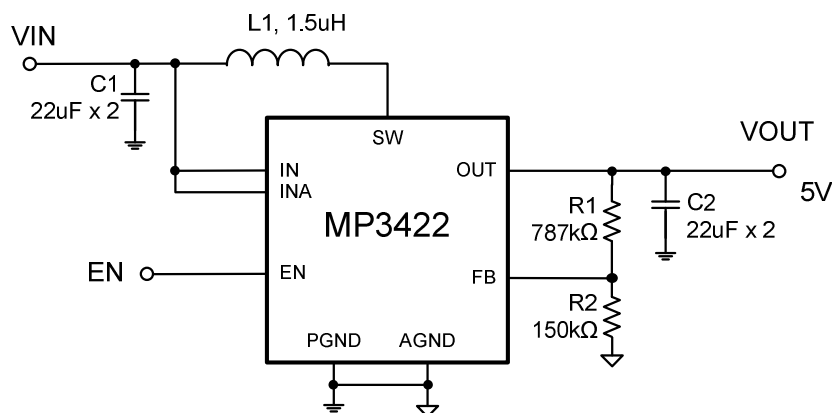
## APPLICATIONS

- Battery-Powered Products
- Power Banks, Juice Packs, Battery Back-up Units
- USB Power Supply
- Consumer Electronic Accessories
- Tablets

All MPS parts are lead-free and adhere to the RoHS directive. For MPS green status, please visit MPS website under Products, Quality Assurance page.

"MPS" and "The Future of Analog IC Technology" are Registered Trademarks of Monolithic Power Systems, Inc.

## TYPICAL APPLICATION



## ORDERING INFORMATION

Part Number*	Package	Top Marking
MP3422GG	QFN-14 (2mmX2mm)	See Below

\* For Tape & Reel, add suffix -Z (e.g. MP3422GG-Z)

## TOP MARKING

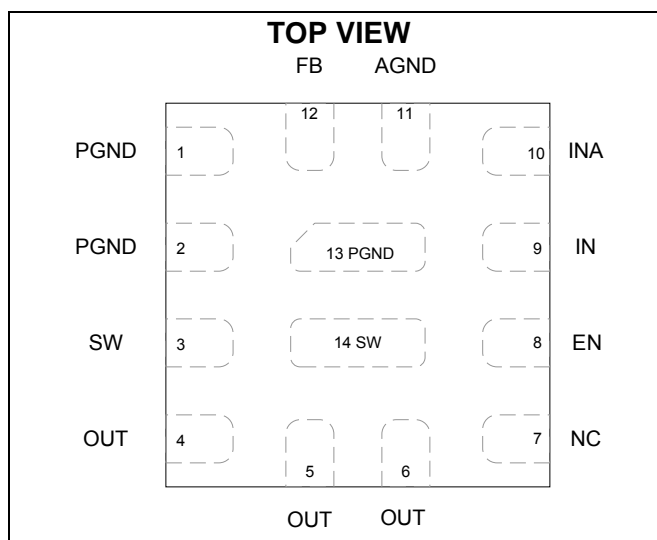
—  
CNY  
LLL

CN: product code of MP3422GG;

Y: year code;

LLL: lot number;

## PACKAGE REFERENCE



## ABSOLUTE MAXIMUM RATINGS <sup>(1)</sup>

SW Pin .....	-0.3V to +6.5V (9V for <5ns)
All other Pins .....	-0.3V to +6.5V
Continuous Power Dissipation (T <sub>A</sub> = +25°C) <sup>(2)</sup>	1.56W
Junction Temperature .....	150°C
Lead Temperature .....	260°C
Storage Temperature.....	-65°C to +150°C

## Recommended Operating Conditions <sup>(3)</sup>

Supply Voltage V <sub>IN</sub> .....	1.9V to 5.5V
V <sub>OUT</sub> .....	2.5V to 5.5V
Operating Junction Temp. (T <sub>J</sub> ). -40°C to +125°C	

Thermal Resistance <sup>(4)</sup>	θ <sub>JA</sub>	θ <sub>JC</sub>
QFN-14 (2mmx2mm) .....	80.....	16 °C/W

### Notes:

- 1) Exceeding these ratings may damage the device.
- 2) The maximum allowable power dissipation is a function of the maximum junction temperature T<sub>J</sub> (MAX), the junction-to-ambient thermal resistance θ<sub>JA</sub>, and the ambient temperature T<sub>A</sub>. The maximum allowable continuous power dissipation at any ambient temperature is calculated by P<sub>D</sub> (MAX) = (T<sub>J</sub> (MAX)-T<sub>A</sub>)/θ<sub>JA</sub>. Exceeding the maximum allowable power dissipation will cause excessive die temperature, and the regulator will go into thermal shutdown. Internal thermal shutdown circuitry protects the device from permanent damage.
- 3) The device is not guaranteed to function outside of its operating conditions.
- 4) Measured on JESD51-7, 4-layer PCB.

## ELECTRICAL CHARACTERISTICS

$V_{IN} = V_{EN} = 3.3V$ ,  $V_{OUT} = 5V$ ,  $T_J = -40^{\circ}C$  to  $125^{\circ}C$ , typical values are tested at  $T_J = 25^{\circ}C$ , unless otherwise noted.

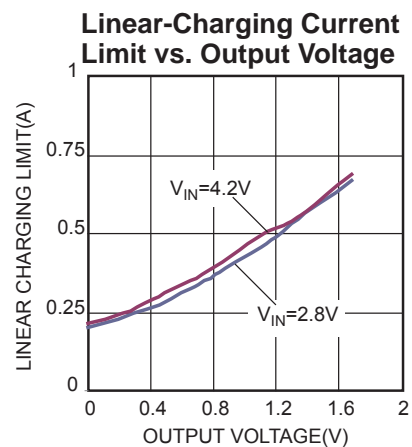
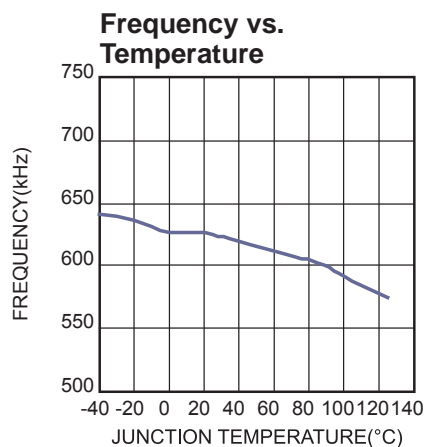
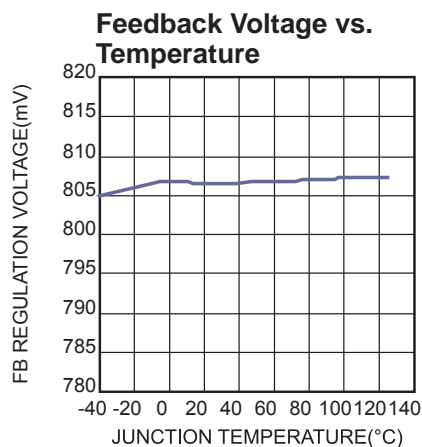
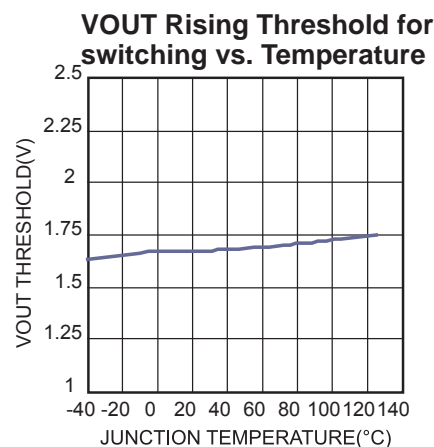
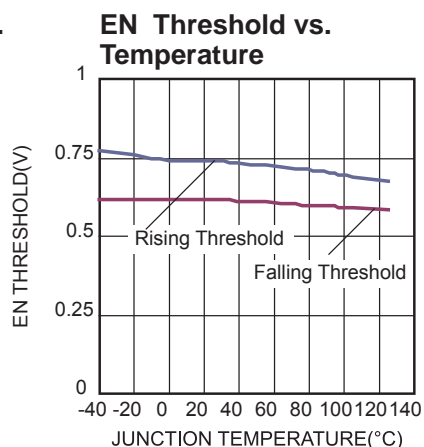
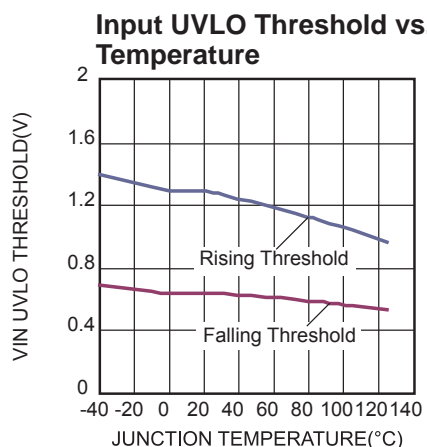
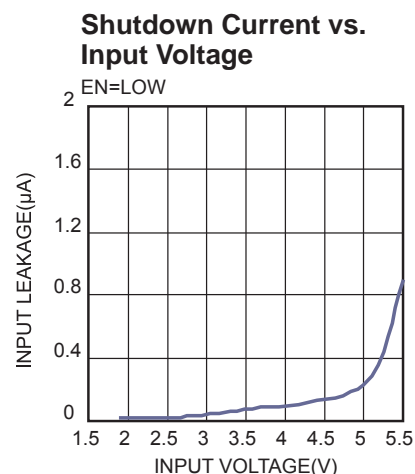
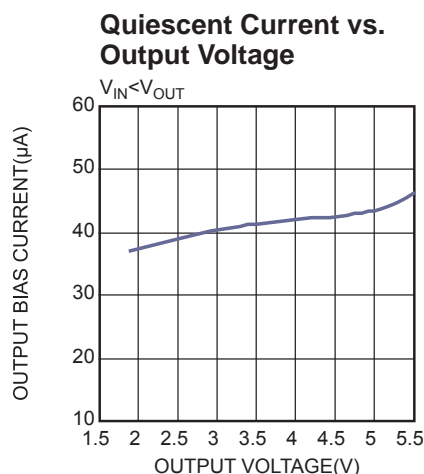
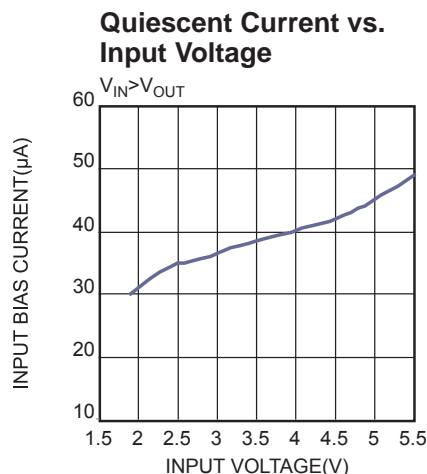
Parameters	Symbol	Condition	Min	Typ	Max	Units
<b>Voltage Range</b>						
Start Operating Input Voltage	$V_{IN}$		1.9		5.5	V
Quiescent Current	$I_{Q\_NS}$	$V_{EN}=V_{IN}=3.3V$ , $V_{OUT}=5V$ , no load Measured on OUT pin, $T_J=25^{\circ}C$		43	57	$\mu A$
		$V_{EN}=V_{IN}=3.3V$ , $V_{OUT}=5V$ , no load Measured on IN pin		0.3		$\mu A$
Shutdown Current	$I_{SD}$	$V_{EN}=V_{OUT}=0V$ , Measured on IN pin, $T_J=25^{\circ}C$		0.1	1	$\mu A$
IN UVLO Rising Threshold	$V_{UVLO\_IN-R}$	$V_{IN}$ Rising $T_J=25^{\circ}C$	1	1.3	1.6	V
IN UVLO Falling Threshold	$V_{UVLO\_IN-F}$	$V_{IN}$ Falling, $V_{OUT}=5V$		650		mV
VOOUT Start Switching Rising Threshold	$V_{UVLO\_OUT-R}$	$T_J=25^{\circ}C$		1.7	1.79	V
<b>Step-up Converter</b>						
Operation Frequency	$F_{SW}$	$T_J=25^{\circ}C$	500	600	700	kHz
		$-40^{\circ}C \leq T_J \leq 125^{\circ}C$	440	600	760	
Feedback Voltage	$V_{FB}$	$T_J=25^{\circ}C$	795	807	819	mV
		$-40^{\circ}C \leq T_J \leq 125^{\circ}C$	791	807	823	
Feedback Input Current	$I_{FB}$	$V_{FB}=850mV$		1	50	nA
NMOS On-Resistance	$R_{NDS\_ON}$			13		m $\Omega$
NMOS Leakage Current	$I_{N\_LK}$	$V_{SW}=5V$		100		nA
PMOS On-Resistance	$R_{PDS\_ON}$			18		m $\Omega$
PMOS Leakage Current	$I_{P\_LK}$	$V_{SW}=5V$ , $V_{OUT}=0V$		0.1		$\mu A$
Maximum Duty Cycle	$D_{MAX}$		90	95		%
Linear Charge Current Limit <sup>(5)</sup>	$I_{CH\_LIMIT}$	$V_{OUT}=1.7V$		0.7		A
		$V_{OUT}=0V$		0.2		A
NMOS Current Limit <sup>(5)</sup>	$I_{SW\_LIMIT1}$	$V_{IN}=5V$ , $V_{OUT}=3.3V$		4		A
	$I_{SW\_LIMIT2}$	Duty=44%, $V_{IN}=2.8V$ , $V_{OUT}=5V$	6.5			A
<b>Logic Interface</b>						
EN High-Level Voltage	$V_{EN\_H}$		1.2			V
EN Low-Level Voltage	$V_{EN\_L}$				0.4	V
EN Input Current	$I_{EN}$	Connect to $V_{IN}$		10		nA
<b>Protection</b>						
Thermal Shutdown <sup>(5)</sup>				150		$^{\circ}C$
Over Temperature Hysteresis <sup>(5)</sup>				20		$^{\circ}C$

### Notes:

5) Guaranteed by characterization, not production tested.

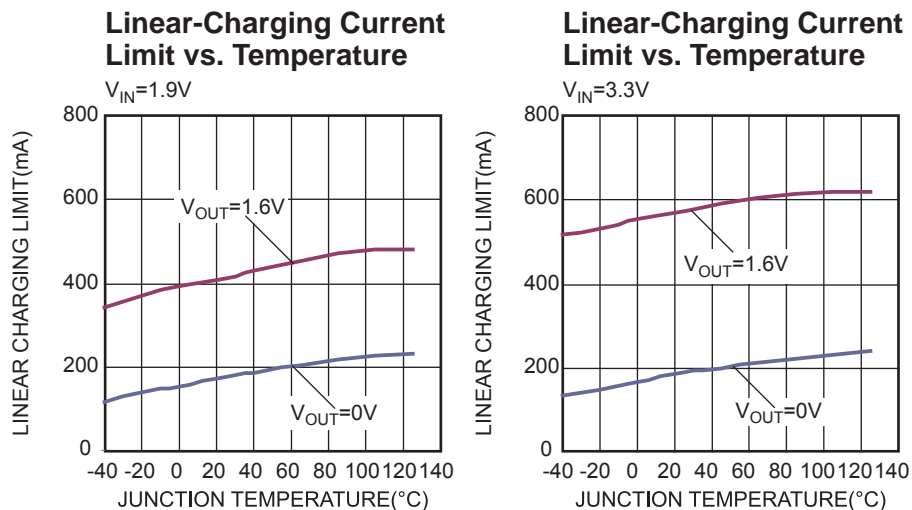
## TYPICAL CHARACTERISTICS

$V_{IN} = V_{EN} = 3.3V$ ,  $V_{OUT} = 5V$ ,  $L = 1.5\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.



## TYPICAL CHARACTERISTICS *(continued)*

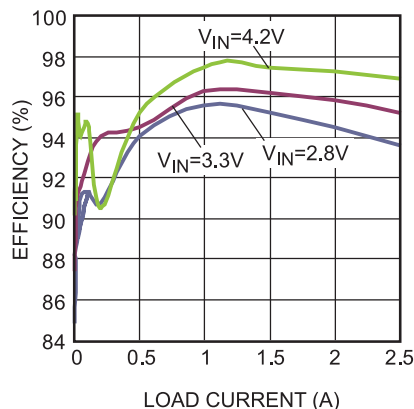
$V_{IN} = V_{EN} = 3.3V$ ,  $V_{OUT} = 5V$ ,  $L = 1.5\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.



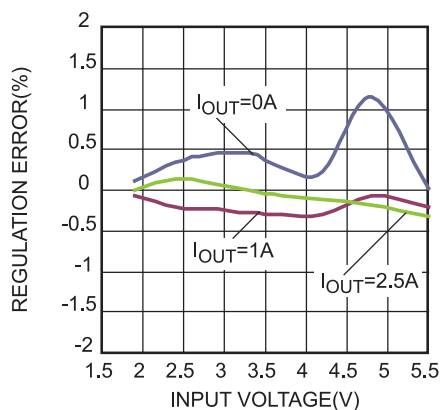
# TYPICAL PERFORMANCE CHARACTERISTICS

$V_{IN} = 3.3V$ ,  $V_{OUT} = 5V$ ,  $L=1.5\mu H$ ,  $T_A = 25^\circ C$ , tested on standard EVB, unless otherwise noted.

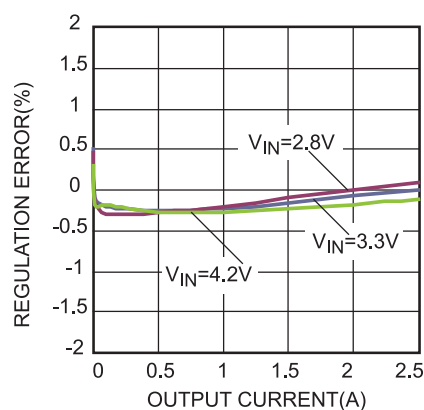
**Efficiency vs. Load Current**



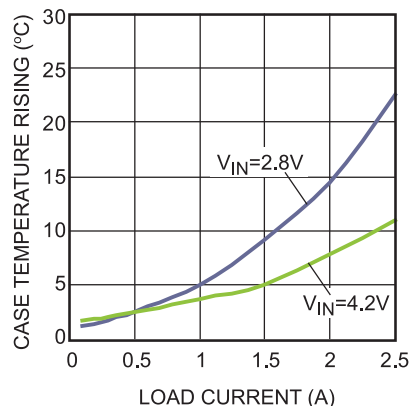
**Line Regulation**



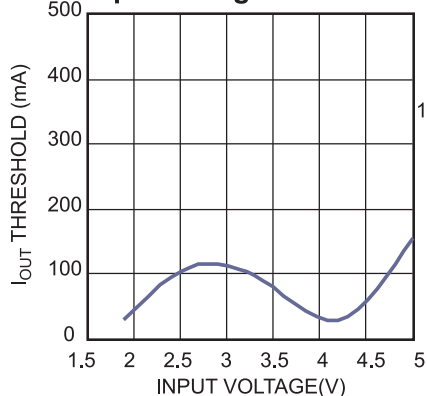
**Load Regulation**



**Case Temperature Rising vs. Load Current**

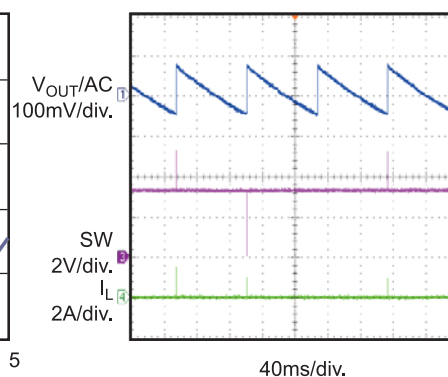


**PSM Threshold vs. Input Voltage**



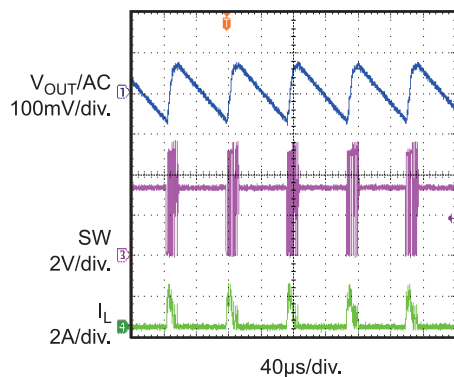
**Output Voltage Ripple**

Load = 0A



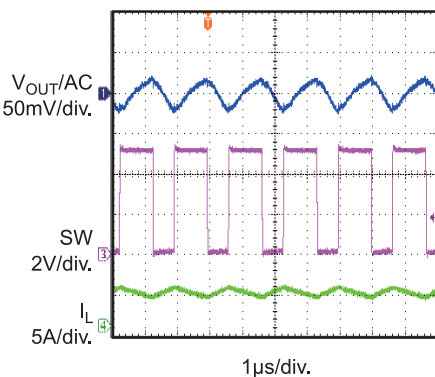
**Output Voltage Ripple**

Load = 0.1A



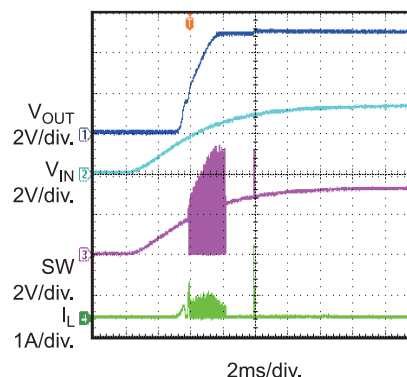
**Output Voltage Ripple**

Load = 2.5A



**$V_{IN}$  Startup**

Load = 0A

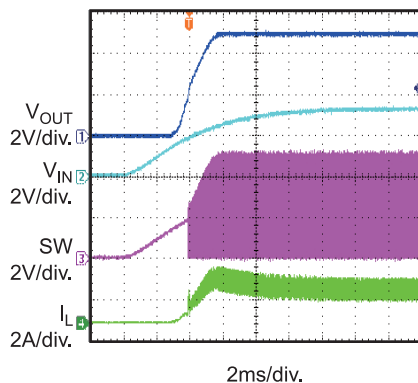


## TYPICAL PERFORMANCE CHARACTERISTICS (continued)

$V_{IN} = 3.3V$ ,  $V_{OUT} = 5V$ ,  $L = 1.5\mu H$ ,  $T_A = 25^\circ C$ , tested on standard EVB, unless otherwise noted.

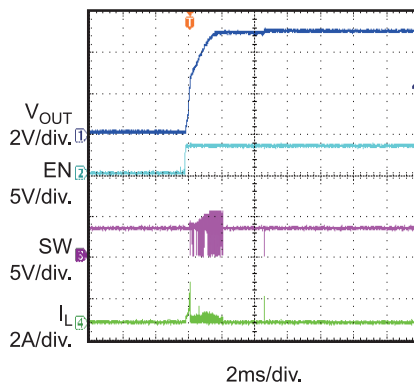
**$V_{IN}$  Startup**

Load =  $5\Omega$



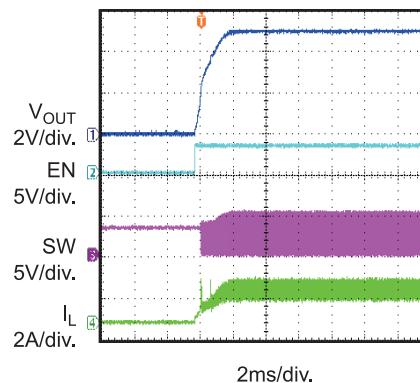
**EN Start up**

Load =  $0A$



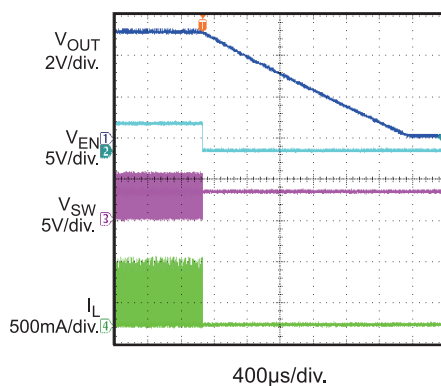
**EN Startup**

Load =  $5\Omega$



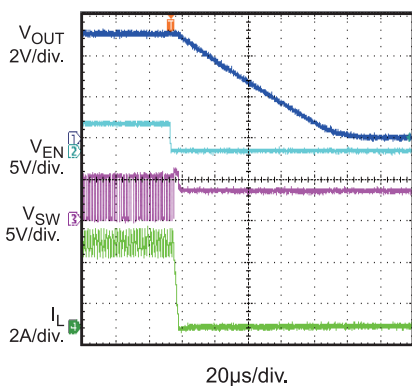
**EN Shutdown**

Load =  $0.1A$



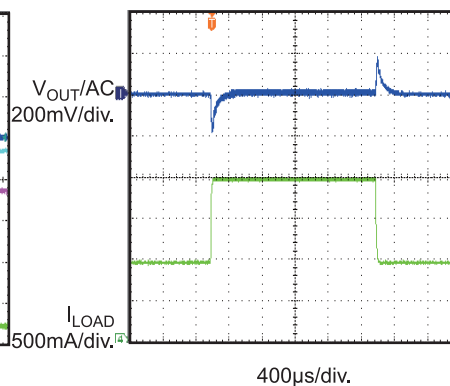
**EN Shutdown**

Load =  $2.5A$



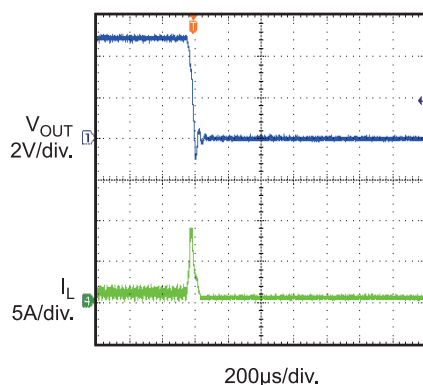
**Load Transient**

Load =  $1A \leftrightarrow 2A$  at  $50mA/\mu s$



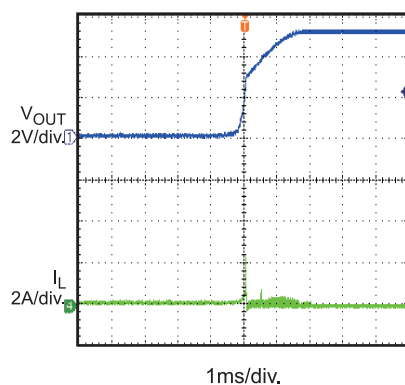
**Short Circuit Entry**

$0.6A$  load to short



**Short Circuit Recovery**

Recover to  $0A$  load

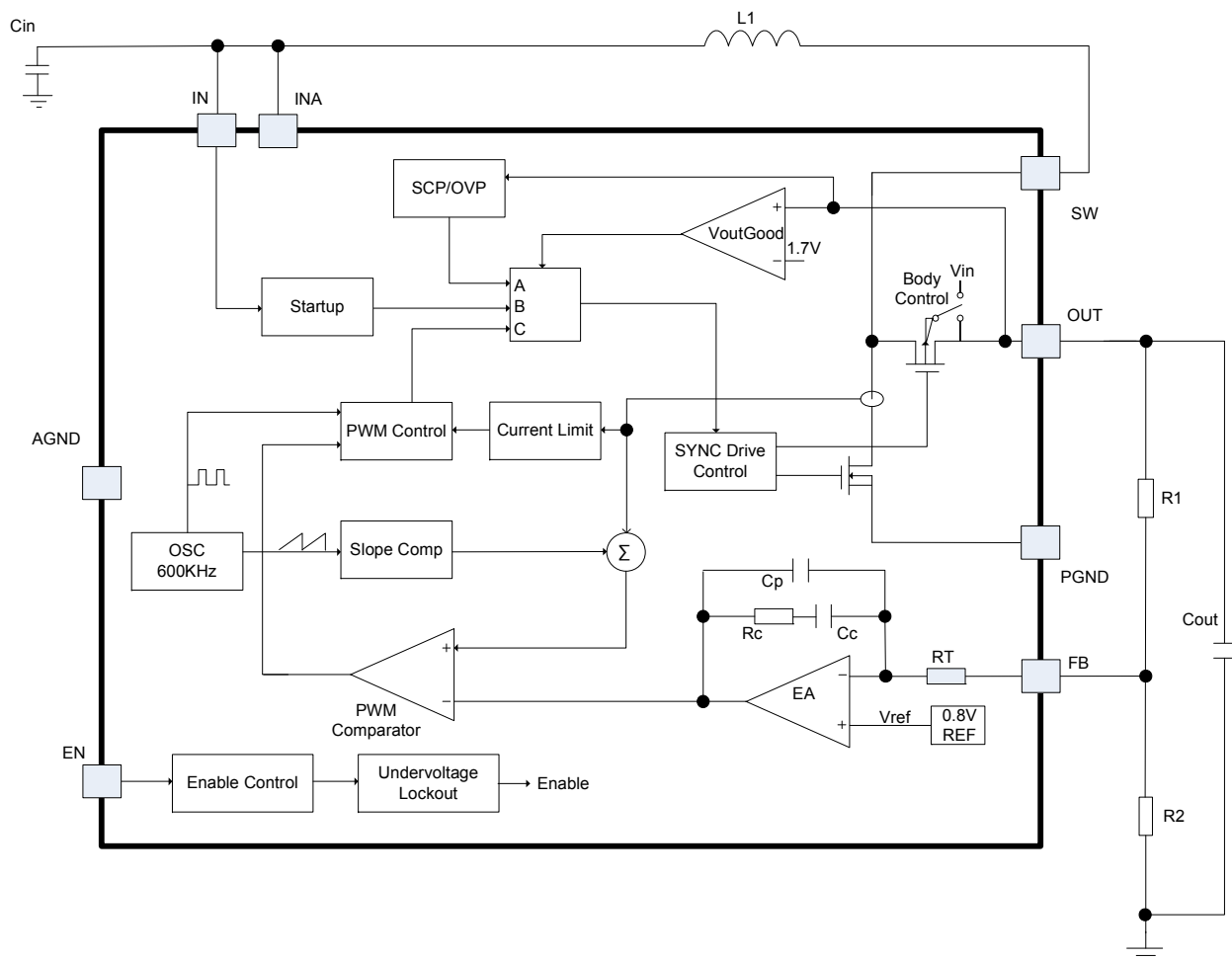




## PIN FUNCTIONS

Pin #	Name	Pin Function
1, 2, 13	PGND	Power Ground.
3, 14	SW	Power Switch Output. SW is the connection node of the internal NMOS switch and synchronous switch. Connect the power inductor between SW and input power. Keep these PCB trace lengths as short and wide as possible to reduce EMI and voltage spikes.
4, 5, 6	OUT	Output Pin. OUT is the drain of the Internal Synchronous Rectifier MOSFET. Bias is derived from OUT when $V_{OUT}$ is higher than $V_{IN}$ . PCB trace length from OUT to the output filter capacitor(s) should be as short and wide as possible. OUT is completely disconnected from IN when EN is low due to the output disconnect feature.
7	NC	No Connect. Reserved for factory use only. Float or connect this pin to GND in the application.
8	EN	Chip Enable Control Input.
9	IN	Power Supply Input. The startup bias is derived from IN. Must be locally bypassed. Once OUT exceeds IN, bias comes from OUT. Thus, once started, operation is completely independent from IN.
10	INA	Power supply input for factory use only, must be connected to IN pin in the application.
11	AGND	Analog Signal Ground.
12	FB	Feedback Input to Error Amplifier. Connect resistor divider tap to this pin. The output voltage can be adjusted from 2.5V to 5.5V

## FUNCTION DIAGRAM



### Figure 1: Functional Block Diagram

## OPERATION

The MP3422 is a 600kHz, synchronous step-up converter with true output disconnect. It is packaged in a QFN 2X2-14 lead package. The device features fixed-frequency current mode PWM controls for excellent line and load regulation. Internal soft-start and loop compensation simplifies the design process and minimizes external components. The internal low  $R_{DSon}$  MOSFETs, combined with frequency stretching operation, enables the device to maintain high efficiency over a wide load current range.

### Start-Up

When the IC is enabled and the voltage on the IN pin exceeds  $V_{UVLO\_in-R}$ , the MP3422 starts up in the linear charge period. During this linear charge period, the PMOS rectifier turns on until the output capacitor is charged to 1.7V. The PMOS current is limited to 0.2A when  $V_{out}$  is 0V to avoid inrush current. While the output ramps up, the PMOS current limit also increases and ramps to 0.7A at 1.7V output. This circuit also helps to limit the output current under short circuit conditions. Once the output is charged to 1.7V, the linear charge period elapses and the MP3422 starts switching in normal closed loop operation. In normal operation, with  $V_o$  lower than  $V_{in}+0.3V$  the MP3422 operates in step down mode with 4A typical peak current limit, and works in boost mode when  $V_o$  is higher than  $V_{in}+0.3V$  with more than 6.5A current limit.

**Table 1: Work Mode during Startup**

$V_{OUT} < 1.7V$	Linear Charge Mode
$V_{OUT} \geq 1.7V \text{ \& } V_{OUT} < V_{IN} + 0.3V$	Down Mode
$V_{OUT} \geq 1.7V \text{ \& } V_{OUT} \geq V_{IN} + 0.3V$	Boost Mode

In down mode, gate of HS-FET is pulled to  $V_{IN}$ , and it works with high impedance when HS-FET is on, the power-loss is high and regulation is bad in down mode. Down mode is designed for work in startup and SCP condition, it is not suggested to set MP3422 in down mode in normal work, unless the thermal and regulation will not affect the system performance.

Once the output voltage exceeds the input voltage, the MP3422 powers its internal circuits from  $V_{out}$  instead of  $V_{in}$ .

### Soft-Start

The MP3422 provides soft-start by charging an internal capacitor with a current source. This soft start voltage continues to rise, following the FB voltage, during the linear charge period. Once the linear charge period elapses, and the voltage on this capacitor is charged, the reference voltage is slowly ramped up. The reference soft start time is typically 2ms from 0V to 0.807V.

The soft start capacitor is discharged completely in the event of a commanded shutdown, thermal shutdown or short circuit at the output.

### Device Enable

Operation is enabled when the EN pin is switched high and placed into shutdown mode when low. In shutdown mode, the regulator stops switching and all internal control circuitry is off. The load is isolated from the input.

### Power Save Mode

The MP3422 will automatically enter power save mode (PSM) when the load decreases and resume PWM mode when the load increases. When the device goes into PSM, it lowers the switching frequency saving switching and driver losses, and switches to pulse skip mode if the load continues to decrease.

### Error Amplifier

The error amplifier (EA) is an internally-compensated amplifier. The EA compares the internal 0.807V reference voltage against  $V_{FB}$  to generate an error signal. The output voltage of the MP3422 is adjusted by an external resistor divider. A voltage divider from  $V_{OUT}$  to ground programs the output voltage via the FB pin from 2.5V to 5.5V using the equation:

$$V_{OUT} = 0.807V \times (1 + R1/R2)$$

Set the value of R1 and R2 to achieve low quiescent current. R1 values larger than 600k are recommended for good stability and transient balance.

### Current Sensing

Lossless current sensing converts the NMOS switch current signal to a voltage which is summed with the internal slope compensation. The summed signal is compared to the error amplifier output to provide a peak current control command for the PWM. Minimum peak switch current limit is 6.5A. The switch current signal is blanked for about 60ns internally to enhance noise rejection.

### Output Disconnect

The MP3422 is designed to allow true output disconnect by eliminating body diode conduction of the internal PMOS rectifier. This allows  $V_{OUT}$  to go to zero volts during shutdown, or isolate and maintain an external bias on  $V_{OUT}$ . It also allows for inrush current limit at start-up, minimizing surge current seen by the input supply. To obtain the advantage of output disconnect, there must not be an external Schottky diode connected between the switch pin and  $V_{OUT}$ .

### Over Load and Short Circuit Protection

When an overload or a short circuit occurs, the output voltage will drop. If  $V_{out}$  drops below  $V_{in}+0.3V$ , the MP3422 will convert to step down mode. If  $V_{out}$  drops below 1.7V, the device will convert to linear charge mode. If  $V_{out}$  drops below about 70% of the nominal output voltage, the MP3422 will immediately shut down and re-start after about 40 $\mu$ s as a new power-on cycle.

### Over Voltage Protection

If  $V_{out}$  is higher than 7V, boost switching stops. This prevents overvoltage from damaging the internal power MOSFET. When the output drops below 7V, the device resumes switching automatically.

### Thermal Shutdown

The device contains an internal temperature monitor. The switches turn off if the die temperature exceeds 150°C. The device will resume normal operation below 130°C.

## APPLICATION INFORMATION

### COMPONENT SELECTION

#### Input Capacitor Selection

Low ESR input capacitors reduce input switching noise and reduce the peak current drawn from the battery. Ceramic capacitors are a good choice for input decoupling and should be located as close as possible to the device. A ceramic capacitor larger than 22μF is recommended to restrain  $V_{IN}$  ripple.

#### Output Capacitor Selection

The output capacitor requires a minimum capacitance value of 22μF at the programmed output voltage to ensure stability over the full operating range. A higher capacitance value may be required to lower the output ripple and also transient ripple. Low ESR capacitors such as X5R or X7R type ceramic capacitors are recommended. Supposing that ESR is zero, the minimum output capacitor to support the ripple in the PWM mode could be calculated by:

$$C_o \geq \frac{I_o \times (V_{OUT(MAX)} - V_{IN(MIN)})}{f_s \times V_{OUT(MAX)} \times \Delta V}$$

Where,

$V_{OUT(MAX)}$  = Maximum output voltage

$V_{IN(MIN)}$  = Minimum Input voltage

$I_o$  = Output current

$f_s$  = Switching frequency

$\Delta V$  = Acceptable output ripple

A 1μF ceramic capacitor is recommended between the Out and PGnd pins. This reduces spikes on the SW node and improves EMI performance.

#### Inductor Selection

The MP3422 can utilize small surface mount chip inductors due to its 600kHz switching frequency. Inductor values between 1μH and 2.2μH are suitable for most applications. Larger values of inductance will allow slightly greater output current capability by reducing the inductor ripple current, but larger value inductance increases component size. The minimum inductance value is given by:

$$L \geq \frac{V_{IN(MIN)} \times (V_{OUT(MAX)} - V_{IN(MIN)})}{V_{OUT(MAX)} \times \Delta I_L \times f_s} \quad (3)$$

$\Delta I_L$  = Acceptable inductor current ripple

The inductor current ripple is typically set for 30% to 40% of the maximum inductor current. The inductor should have low DCR (series resistance of the inductor current without saturating windings) to reduce the resistive power loss. The saturated current ( $I_{SAT}$ ) should be large enough to support the peak current.

#### PCB Layout Considerations

PCB layout for high frequency switching power supplies can be critical. Poor layout can result in reduced performance, excessive EMI, resistive loss and system instability.

The steps below ensure good layout design.

1. The output capacitor must be placed as close as possible to the OUT pin, with minimal distance to PGND. A small decoupling capacitor should be paralleled with the bulk output capacitor and placed as close as possible to the OUT Pin. This is very important to reduce the spikes on the SW Pin and improve EMI performance.
2. The input capacitor and inductor should as close as possible to the IN and SW pins. The trace between the inductor and the SW pin should be wide and as short as possible.
3. The feedback loop should be far away from all noise sources such as the SW pin. The feedback divider resistors should be as close as possible to the FB and AGND pins.
4. The ground return of the input/output capacitors should be tied as close as possible to the PGND pin with a large copper GND area. Vias around the GND pin are recommended to lower the die temperature.
5. INA pin must be connected to IN. NC pin can either float or be connected to GND.

Figure 2 recommends components placement for MP3422.

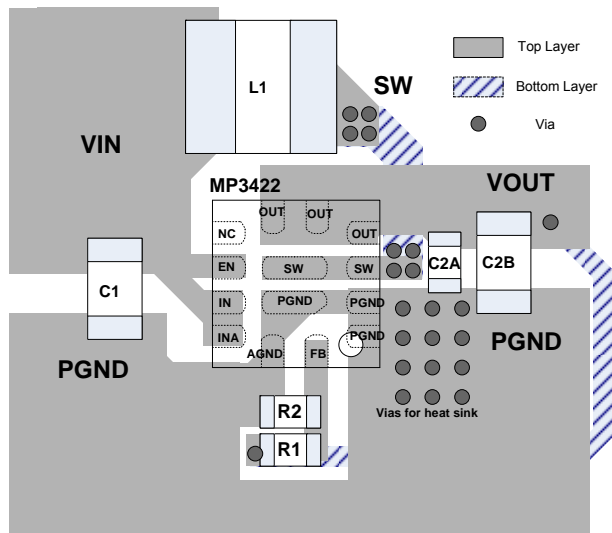


Figure 2, Layout Recommendation

## Design Example

Below is a design example following the application guidelines for the following specifications:

Table 2: Design Example

$V_{IN}$	2.8V-4.2V
$V_{OUT}$	5V
$I_{OUT}$	0A-2.5A

The typical application circuit for  $V_{OUT} = 5V$  in Figure 3 shows the detailed application schematic, and is the basis for the typical performance waveforms. For more detailed device applications, please refer to the related Evaluation Board Datasheets.

## TYPICAL APPLICATION CIRCUITS

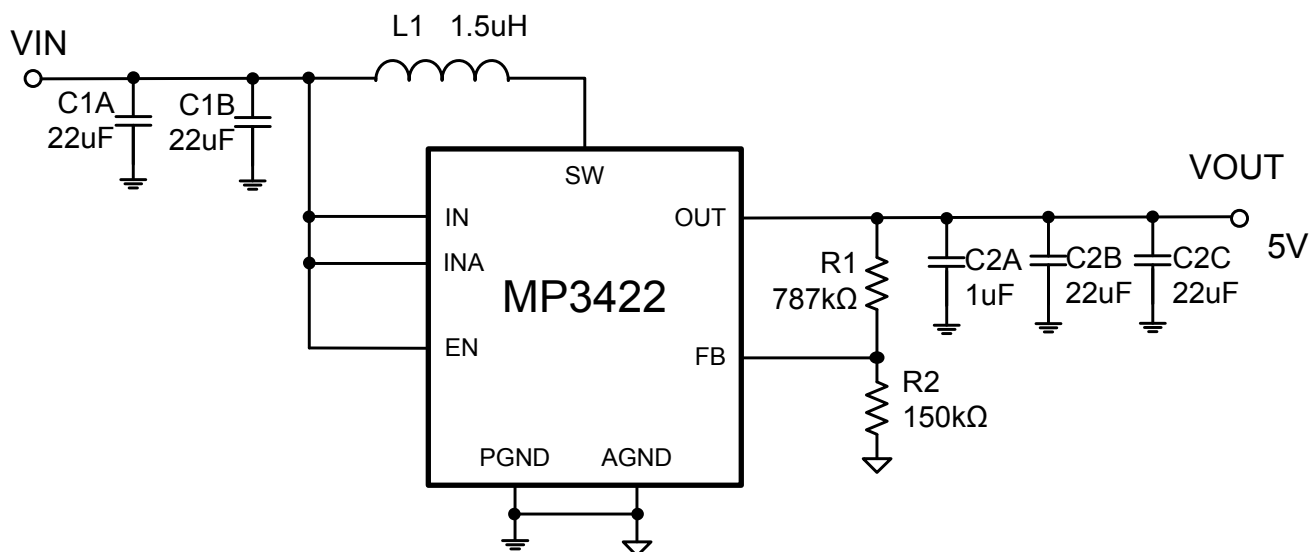
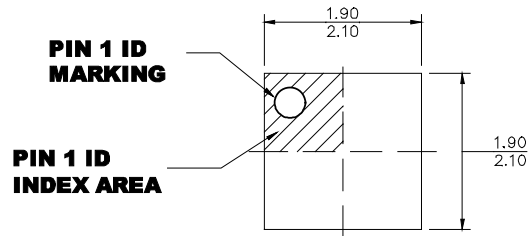


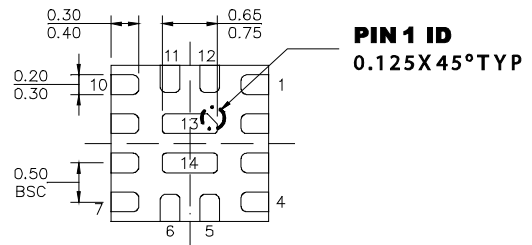
Figure 3, Typical Boost Application Circuit,  $V_{IN}=2.8V$  to  $4.2V$ ,  $V_{OUT}=5V$ ,  $I_{OUT}=0A-2.5A$

# PACKAGE INFORMATION

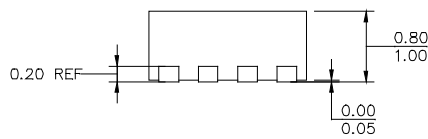
## QFN-14 (2mmX2mm)



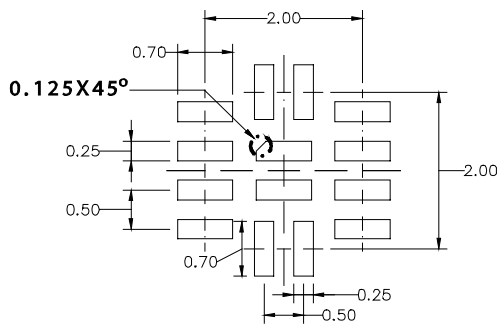
**TOP VIEW**



**BOTTOM VIEW**



**SIDE VIEW**



**RECOMMENDED LAND PATTERN**

## NOTE:

- 1) ALL DIMENSIONS ARE IN MILLIMETERS.
- 2) EXPOSED PADDLE SIZE DOES NOT INCLUDE MOLD FLASH.
- 3) LEAD COPLANARITY SHALL BE 0.10 MILLIMETERS MAX.
- 4) JEDEC REFERENCE IS MO-220.
- 5) DRAWING IS NOT TO SCALE.

**NOTICE:** The information in this document is subject to change without notice. Users should warrant and guarantee that third party Intellectual Property rights are not infringed upon when integrating MPS products into any application. MPS will not assume any legal responsibility for any said applications.